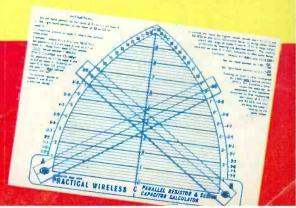
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Practical 2

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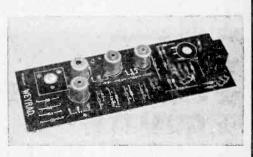
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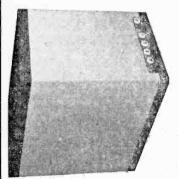
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Separate bass and treble "cut" and "boost" controls. Twin separately controlled inputs so that controlled inputs so that two instruments or mike" and pick-up can be used at the same time. Two loudspeakers are incorporated, at 21n. high flux 14 watt bass unit. and a 6 x 4in. elliptical for treble. Cabinet is well made and finished as Junior Model. Size approx. 18 x 18 x 81n. Only 15 GMS Carr.

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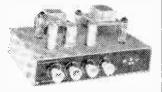
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300-0-300v. 100mA. 6.3v. 4a, 0-5-6.3v. 3a 26/9
300-0-300v. 100mA. 6.3v. 4a, 0-5-6.3v. 3a 26/9
350-0-350v. 100mA. 6.3v. 4a, 0-5-6.3v. 3a 29/9
425-0-4250v. 100mA. 6.3v. 4a, 0-5-6.3v. 3a 29/9
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Consisting of three transistor amplifiers, recordplay, Volume control, miniature speaker, forward-stop-rewind switch, reel of tape and spare reel, motor, attractive coloured case, Mic. and earphone sockets, pick-up coll, mike, earphone and carrying handle suppiled. Standard battery operated. Simple to put together in less than one hour. Brand new and guaranteed. Exclusively offered complete with all accessories but only \$44.19.6. No extras to buy.

technicians
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D.C. voltage:
(0-15-150-1,000 v. (1,000 o.p.v.)).
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G-15-150-1.000 v. (1.000 o.p.v.).
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Size: 31 x 21 x 1in.
Complete with battery, test
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12v. input, 500v-output at 65 mA. or 6v. input, 250 output at 75 mA. Only

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Precision engineered Magnetic Microphonefor lapel or hand use. Only 14in. diameter. Exceptionally sensitive. Chrome plated case.

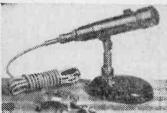
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5ft. shielded cable. Only 12/6.

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harmonics from a built in miniature transistor oscillator. Push button operation, and battery strength indicator. Ideal for making rapid checks on radios. amplifiers. TV Tuners. etc. A must for the amateur, hobbyist and service man. PRICE 42/6. Complete with batteries. 3-WAY SLIM CRYSTAL MICROPHONE

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MAIL ORDERS TO (DEPT. P.), 32a COPTIC STREET. May be hand-held, stand mounted (either floor stand or desk stand) or suspended by lavalier cord. Response Response 60-10.000 cps. 60-10.000 cps.
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Switch. Output
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Omni-directional head.
Cilps on or off
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mitting tilting for multi-angle use. Satin chrome Supplied complete with desk stand shielded cable, lavaller cord. ONLY

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This most famous Army Trans/Receiver covers 2-3 Mc/s. (150-37 metres in two bands). Has an intercom. amplifier. Designed for 12 and 23 volt operation but supplied with "P.W." Mains conversion details. Uses a 6 valve superhet receiver. 1.F. being 465 Kc/s, and a 6 for volce and C.W. operation. Incorporates test and tuning meter for voltages, aerial loading and current tests. Panel Controls: Frequency tuning. P.A. tuning. Gain control. MCW, CW, R/T switch. Het-tone netting, Off-on Quench aerial, AVC LT-HT—Drive tests. Supplied complete with valves and instruction book. Only 65/r. Carriage 10/r.

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TAKE-OVER BID MAKES THIS FANTASTIC OFFER POS-SIBLE—the beautifully compact "5-STAR VOLKSRADIO"

measuring 4% x 2% x 14in. Perfect personal earphone reception-in the Bedroom, Office, Garden-over all medium waves (incl. Luxembourg). Under Id. hour running cost. ANY-ONE can assemble it in one or two hours using our simple A.B.C. plan. Complete set of parts ONLY 14/11, plus 2/6 P. & P. C.O.D. extra. (Parts can be bought separately.) Money Back Guarantee.



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Build this newly-designed "MINUETTE" 4-STAGE transistor set in very strong ready drilled ULTRA-MODERN CASE, size only 8 x 3 x 1 ln. Uses three transistors and dlode and SELF-CONTAINED LOUISPEAKER, Very

CONTAINED LOUDSPEAKER. Very sensitive, ideal for office, bedroom, holidays, etc. Months and months of listening off a 1/2d. Lattery. Can be built FOR ONLY 39/6, including PROPER OASE, ministure speaker, etc. SIMPLE AS A.B.O. PICTORIAL STEP-BY-STEP PLANS etc., pins STEP-BY-STEP PLANS etc., pins passed and packing 1/3 (C.O.D. 2/passed) parts list. 1/4 sold separately, priced parts list 1/-



39/6



Revolutionary INTERNAL FERRITE AERIAL Makes this sensational pocket-size radio the best money-saving bargain of all time. Powerful. superb tone and clarity, ensures perfect reception for all your favourite programmes

Completely portable, only 51 x 8 x 1 in. Two-tone case. Anyone can assemble with our simple PRINTED CIRCUIT PLAN. Send 37/6, plus 2/6 P. & P. (C.O.D. 2/extra), Satisfaction guaranteed. (All parts available separately).

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Unbellevably small—Outrageously cheap. You will be amazed at the fine quality of tone and volume of this great little radio. Only a fantastic $3\frac{1}{2} \times 2\frac{1}{2} \times 1\frac{1}{2} \ln$, the MiAMI will bring you great entertainment for months on a 1/2d, battery, Simple assembly plan with each set. ONLY 32/6. YES 32/6!

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This is a pocket 2-stage translator set not much larger than a matchbox. Excellent clear reception covering all medium waves, works for months off a tiny 1½ or 3 volt battery costing only 8d. Easy to build and an on a tiny 1% of 3 wolt battery costing only 8d. Easy to build and an excellent introduction to translstor circuitry. Everything can be supplied down to the last nut and bolt incl. SIMPLE PICTORIAL STEP-BY-STEP PLANS FOR ONLY 19/6. plus post ami packing 1/6. (C.O.D. 2/-extra). Farts sold separately, priced extra). Part



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As featured on Radio Luxembourg-The "San Remo" 6 Star covers all medium waves including "Home", "Light", etc. Reliable and lightweight-Slips easily into the Pocket or Handbag-size only 4! x 21 x 14in. Works for Months on 1/2d. Battery!

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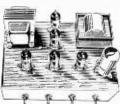
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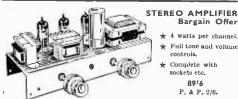
10/14 WATT HI-FI AMPLIFIER KIT

A stylishly finished monaural amplifier with an output of 14 watts from 2 El.84s in push-pull. Super reproduction of both music and speech, with negligible hum. Separate inputs for mike and gram allow records and announcements to follow each other. Fully shrouded ultra output transformer shrouded uitra output transformer to match 3-15 speaker and 2 inde-pendent volume controls, and separate bass and treble controls are provided giving good lift and cut. Valve line-up 2 ELS4, ECCS3, EF86 and EZ80 rectifier. Simple instruction booklet 1/6. (Free with parts.)





ONLY £6.19.6 P. & P. 6/6.



Bargain Offer

- # 4 watts per channel.
- Full tone and volume
- controls. Complete with

sockets etc. 89/6

P. & P. 2/6.

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AMPLIFIER ON PRINTED CIRCUIT BOARD

Two valve. UY85, UL84 O.P. trans., use with 80 voit tap off motor. 89/6.
P.P. 2/6 on above. Dropper res. for filaments if required. 2/6.

B.S.R. AUTO UNITS 160 v. Suitable for use with above, (Slightly soiled.) 24.4.0. P. & P. 5/-.

LARGE CABINET

Suitable for above two items. Complete with 3 ohm speaker. 23.9.6. Carr. 5/5.

Superior CABINET similar to above to take 8 x 5in. speaker, with motor board, will accommodate BSR UA14 or UA16. 23.9.6. Carr. 5/6. Speaker 15/- extra. P. a P. 1/6 extra.

BRAND NEW 3 OHM LOUDSPEAKERS

24in. 12/6; 5in. 12/6; 64in. 15/-; 10in. 21/-; 12in. 27/6. Goodmans 5in. tweeter 10/6 E.M.I. 24in. tweeter, 10/6 Goodmans 10in. x 6in. 22/6 E.M.1. 131in. x 81in. high flux 32/8 Rola Celestion approx. 9in. x

6in, middle register speaker 10/6 Also 15 ohm 12in., 30/-P. & P. 1/6 per speaker.

4-SPEED PLAYER UNIT BARGAINS

SINGLE PLAYERS TU/12. £3.10.0. AUTO CHANGERS

B.S.R. UA14, 26.2.6. Latest B.S.R. UA16, 27.2.6. Latest Garrard "Auto-Slim" 26.17.0. Carr. 5/on each.

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P.V.C. base, full frequency L.P. tape. 7in., 1800ft. (normally 50/-) 27/6; 52in., 1,200ft. (normally 55/-), 18/9. P. & P. 1/- per spool. Ideal for 2 or 4 track recorder.

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B.S.R. MONARDECK (Single speed) 33in. per sec., simple control, uses 53in. spools, 26.15.0 plus 5/6 carr. and ins. (Tapes plus 5/6 carr. and ins. (Tapes extra on both).

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2 valve, A.C. mains, 3 watts output, ready built, tested and complete with valves and output transformer. Size 7in. w. x 2½in. d. x 5½in. h. 55/- P. & P. 3/-.

Suitable speakers: 6in. 15/- or 10 x 6in. 22/6. P. & P. 1/6 on each,

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MAINS TRANSFORMER. Impregnated and fully shrouded. Size 4½ x 3½ x 2½in. Weight 6 lbs. Tapped primary 205, 225, 245 v. Electrostationscreen. Output 3000-0300 v. at 120 m/a D.C. plus 1050 v. half wave at 3 m/a

D.C. 6.3 v. at 3.5 amps, centre tapped 5 v. at 23 amps and 0.5 v. at 4.6 amps. PRICE ONLY 21/c each, P. & P. 5/c.
CARBON MIKE INSERTS, Brand new, 21/n. dla., 3/6. P. & P. 9d.
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Brand new and naused. Brand new and nnused, Complete with PCC84 and PCF80 valves. 34-38 Mc/s I.F. Biscuits for Channels 1 to 5 and 8 and 9, Circuit diagram supplied.

ONLY 25/- each. P.P. 2/6.

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A permeability typed type head by a famous maker, supplied without valve spindle, 18/6, plus 1/9 P. & P. Valve 8/6 extra. Drum and spindle 3/6 extra.

E.M.I. 4-speed Player and P.U.

FURTHER HUGE PURCHASE enables us to offer these 67/6 P. & P. at 4/6. 4/6.



Heavy 8½in, metal turn-table. Low flutter per-formance 200/250V shaded motor with tap at 45V for amplifier valve filament if required. Turnover LP/78 head.

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Complete with leatner personal earphone Will case, personal earphone and PP3 battery. Will receive Luxembourg etc. loud and clear.

SIX TRANSISTOR TYPE Size 4 x 2½ x 1½in. 24.19.6.

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Size 4; x 2; x 1; in. £5.19.6. Both plus P. & P. 2/6.

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Heavily woven in champagne and brown, 48in, wide, Originally 35/- per yard length.

OUR SPECIAL PRICE 12/- per yard length.
P. & P. 1/6. Also Red Rexine. Dark Grey and Oatmeal fabrics for cabinet covering, 54in, wide, 13/6

covering, 54in. wide, 13/6 per yard length. P. & P. 1/6.

HARVERSON'S F.M. TUNER Mk.I

F.M. uning head famous maker 9999999 • Guaranteed non-drift, Per-meability tuning.

• Frequency coverage 88-100 Mc/s. • OA81 balanced diode output. had mc/s. OA81
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Mark III Version as Mark I but with output stage (ECLE2) and tone control. 27.7.0. P. 8.6.
Handsome Metal Cabinets, Choice of Grey, Black or Green, To lit Mark I, 25/r, F. & F. 2/6.
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6 TRANSISTOR AND DIODE SUPERHET

first-class 2 waveband A first-class 2 waveband transistor superhet in kit form. Printed circuit panel (size 8½ x 2½n) @ 3 pre-aligned, I.F. transformers. High-gain Ferrite rod aerial. @ All First-grade transistors. @ Car aerial winding. @ Push-pull output. @ All parts supplied with simple instructions.

All parts sold separately

ONLY **£4.5.0** P. & P.

21in. 35 ohms speaker, 10/6; 211a. 35 ohms speaker, 10/6; 31in. 35 ohms speaker, 16/6; 35 ohms 5in. P.M., 18/6; 7 x 4in. 35 ohms speaker, 21/-. P. & P. 1/6 per speaker.

Portable CABINET

Size approx. 9½ x 6½ x 3½in. Suitable for above using 3½in. speaker. 25/-, P. & P. 2/-.

COIL AND TRANSFORMER SET FOR TRANSISTOR SUPERHET

3 I.F. transformers, one oscillator coil, one driver transformer and wound Ferrite aerial (med., long and aerial coupling), 28/6 complete, post 1/- ii transistor printed circuit, board to match, 8/8. post 9d. Circuit diagram 1/6 extra.

QUALITY RECORD PLAYER **AMPLIFIER**

A top-quality record player amplifier. This amplifier (which is used in a 29 gn. record player) employs ECCS3, EL84, EZ50 valves. Bass, trebie and volume, Un/off controls.

PRICE 69/6 P. & P. 3/6

DITTO. Mounted on board with output transformer and 64 in. speaker. Complete at 89/6, P. & P. 4/6

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GET15 (Matched Pair) 15/-.. 5/-PX A101 X A103 V15/10p 6/-OC76 ... 6/- V10/10p ... 12/8 Set of Mullard 6 transistors 25/-. Set of G.E.C. 1,874; 2873; 3, 81 or GET114, 20/-. All Post Free.

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MULLARD 3-VALVE PRE-AMPLIFIER TONE CONTROL UNIT

Designed mainly for Mullard
Range of Amplifiers, also suitable
for any Amplifier requiring input up
to 250mV. Incorporates 5 input
Channels, including for Tape and Magnetic
Pickups. Separate Bass and Trable controls.
High pass filter 20 to 160 c/s, low pass filter



5-9 Kc/s. Totally enclosed in case size 111 x 41 x 41. KIT OF PARTS £10.0.0

ASSEMBLED & TESTED £13.13.0

MULLARD "5-10" MAIN AMPLIFIER



For use with MULLARD 2-stake pre-amplifier with which an undistorted power output of up to 10 waters is obtained. SPECIFIED COMPONENTS AND MUL-LARD VALVES including PARMEKO MAINS TRANSFORMER and choice of PARMEKO or PARTRIDGE Output Transformer. COMPLETE KIT

(Parmeko Output Trans.) ASSEMBLED AND TESTED

£10,0,0 £13.10.0

ABOVE incorporating PARTRIDGE OUTPUT TRANS. £1.6.0 extra.

THE MULLARD 510/RC AMPLIFIER

The popular complete "5-10" incorporating Control Unit providing up to 10 watts high quality reproduction. Specified components and new MULLARD VALVES, Includes FERMEKO MAINS TRANS-TRANS-AMENICAL COMPLETE STANDARD OF PARTRIDGE Output Transformers, KIT \$12.0.0

ASSEMBLED £16.0.0 With PARTRIDGE OUTPUT TRANS, £1.6.0 ex.

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A HIGH QUALITY AMPLIFIER DEVEL-OPED FROM THE VERY POPULAR 3-WATT MULLARD "3-3" DESIGN. KIT OF PARTS £8 8 0 £8.8.0

ASSEMBLED AND TESTED Complete to the MULLARD specification including PARMEKO OUTPUT TRANSFORMER. Switched inputs for 78 and L.P. records plus a Radio position. Extra power to drive a Radio Tuning Unit is also available.



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A small Amplifier of genuine high quality performance. Incorporates new MUL-LARD ECL35 Valve, separate BASS and TREBLE controls and produces up to 3 watts undistorted output.

Kit of Parts £4.10.0 Assembled £6.0.0

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Perfectly suited for Portable Installations for which purpose we offer PORTABLE CASE (£3.10.0) the AMPLIFIER (Kit) and 8° x 5° SPEAKER (£1.0.0). All for £9.0.0

£10.0.0

Alternatively with ASSEMBLED AMPLIFIER

The Case quoted above will accommodate some 4-speed Single Record Units. A larger model is available for extra 10⁻. With this Equipment a COMPLETE PORTABLE RECORD PLAYER can be built for £14.0.0



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Self powered Cathode follower output. Incorporates two inputs for CRYSTAL MICROPHONES one for CRYSTAL PICKUPS and a fourth for Radio or Tape. KIT OF PARTS \$8.8.0

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!! SENSATIONAL BARGAINS!!
ABULK PURCHASE ENABLES US TO OFFER THESE TWO GRUNDIG
MODELS AT APPROX. HALF PRICE. Each are Fully Guaranteed.
THE GRUNDIG "MINI-BOY"

THE "LITTLE" SET with "BIG" PERFORMANCE LIST PRICE IS



£10.10.0 \$10.10.0 INCLUDING SPEAKER ENCLOSURE
A six Transistor (plus two Diodes) Portable covering the Medium
Waveband. Small enough to slip into Handbag or Pocket (4" x 2); x 1")
but when at home "big set" performance is obtained simply by slipping
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MULLARD'S 2-VALVE PRE-AMPLIFIER TONE CONTROL UNIT

Employing two EF86 valves and designed to operate with the Mullard MAIN AMPLIFIER but also periectly suitable for other makes.



★ Equalisation for the latest R.I.A.A. characteristics. ★ Input for Crystal Pick-ups and variable reluctance magnetic

types.

Input (a) Direct from High Imp. Tape Head. (b) From a Tape Amplifier or Pre-Amplifier.

Sensitive Microphone Channel. * Wide range BASS and TREBLE Controls. KIT OF £6.6.0 ASSEMBLED AND TESTED £9.10.0

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GOODMANS "AXIETTE"	£5.5.0
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WHARFEDALE "SUPER 8/RS/DD"	£6.14.0
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LEAK "TI/12 PLUS" POWER AMPLIFIER with the "POINT ONE PLUS" PRE-AMPLIFIER, 14 watts rated output...
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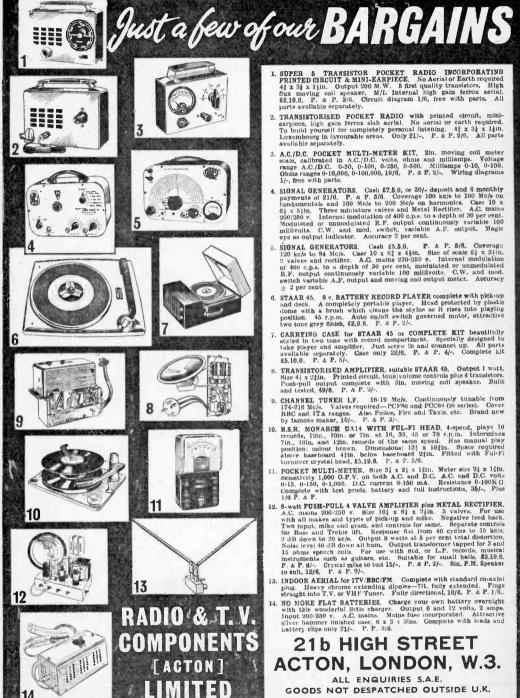
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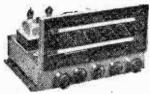
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Tape Amplifier for B.S.R. deck, printed circuit ready wired, with	
Tape Amplifier for B.S.R. deck, printed circuit ready wired, with ECO33, ECL*2, EM85 and EZ81. Complete with all plugs, sockets, panels, knobs, etc. The whole amplifier mounts on to the deck, making a self-contained unit. 28.8.0	
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Case with 7m. x 4m, speaker, in two tone grev 24.4.0	Deposit £1.18.6 and 12 monthly
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The above recorder can be supplied assembled, tested and complete with tape and interophone for £25,0.0 Deposit £2,1.0,0 and 12 monthly £2.1.6	Case with 9in. x 5in. speaker £5.5.0 Complete Kit 4 track Collaro Deposit £3.10.0 and 12 monthly £2.18.2 Tape Pre-amplifier for Collaro deck, with power supplies, ECC83,
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control and input manels mains and output transformers.	au equalised output of 400 m/Volts Half Track
Complete with valves, knobs, plans, screws, etc. EF86, ECC83, EM84, EZ81, OA81 and 2 EL84, 3 watts output.	Quarter Track £9.9.0
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Case for above including 9:n. x 5:n. speaker	EA 4.0
Total Kit as above £29.0.0 Deposit £2.1s.9 and 12 monthly £2.8.2	Marriott 2 track type R/RP/1 Record/Prayback only with bracket
We can outer the above recorder, complete with tape and nacro- phone, in a De Luxe two tone grey cabinet, assembled for £35.0.0	Pressure pad (studio deck only) 4/0 Rrenell Mk, 5 deck, 1 track, 4 speeds 229.8.0
Deposit £3,10.0 and 12 monthly £2.18.2	100 Stimin deck. Read and read 140 1
This Machine is listed at 39 gns, by makers and is a very good buy. Building instructions available at 2/6 each kit (refunded it kit bought)	
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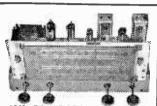
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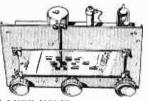
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for transistor circuits, 101- each.
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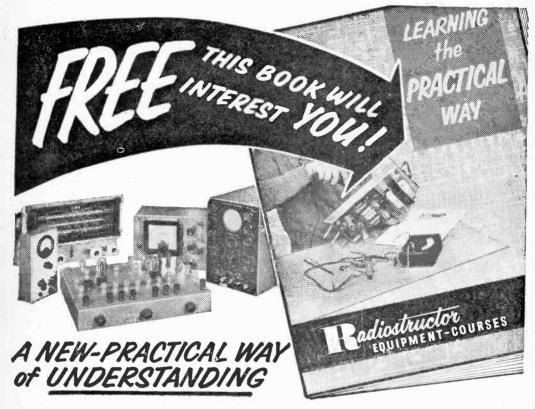
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Practical Wireless

Vol. XXXVIII No. 674 APRIL. 1963

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■ Twin-unit Two !!!? 量
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At Your Service

VERY month we receive many hundred letters from readers wishing to use our Query Service. Most of these are dealt with to mutual satisfaction, but it is only to be expected that with such a vast quantity of mail, readers are sometimes disappointed. We feel it would be useful, then, to outline the nature, purpose and scope of the service.

It is designed primarily to answer queries on articles published in the magazine and to deal with problems which cannot be solved by reference to text books, etc. It involves us in considerable time and expense and for this reason alone it can only be run efficiently if unnecessary time wastage is avoided.

What we CANNOT do

Supply circuit diagrams or blueprints other than those listed every month on the inside back cover page.

(2) Design equipment, or supply circuits and wiring diagrams, to individual requirements. We cannot undertake to run a design service.

(3) Answer queries on most imported equipment, because technical information is often almost completely lacking.

(4) Supply details for converting war surplus equipment.

(5) Answer technical queries over the telephone.

What we CAN do

(1) Deal with queries relating to published articles.

Try to help in technical problems where reference to standard books has not provided a solution.

(3) Give general advice.

(4) Try to help in servicing problems.

What YOU can do

(1) All queries must be accompanied by the query coupon from the current issue.

(2) A stamped and addressed envelope must accompany

the query.

(3) Give clear and concise relevant information on the particular problem.

(4) Avoid "portmanteau" queries.

Failure to observe (1) and (2) will generally fail to elicit a reply. The provision of inadequate data may lead to delays. But delays may also occur through the necessity to locate some obscure facts arising from a query. And, of course, with such a large mail, correspondence does sometimes go astray.

Our whole purpose is to help readers in their problems; on the other hand it should be borne in mind that we offer a free service and not a right to make excessive demands (see item 4).

These notes are intended to help you to obtain the best service and for us to provide it!

Our next issue dated May will be published on April 5th.



NEWS AT HOME AND ABROAD

Broadcast Receiving Licences

THE following statement shows the approximate number of Broadcast Receiving Licences in force at the end of December, 1962, in respect of wireless receiving stations situated within the various Postal Regions of England, Wales, Scotland and Northern Ireland. The numbers include Licences issued to blind persons without payment.

Region				
				Total
London				614,435
Home Counties				571,385
Midland	• •			413,784
North Eastern				435,333
North Western				374,203
South Western				337,679
Wales and Border (countie.	es		188,450
Wets! Dowland			-	
Total England and	Wales			2,935,272
Scotland				308,584
Northern Ireland	• •			105,557
Grand Total			_	3 3/0 /13

More Experimental Stereophonic Transmissions

ON 13th January this year the BBC commenced its second series of field trials of the Zenith-GE stereophonic system using the Wrotham Third Programme transmitter on its normal frequency of 91·3Mc/s.

There are transmissions programmes each week on Sundays at 10 to 10.30, on Wednesdays at 11 to 11.30 and on Saturdays at 11 to 11.30.

During the five minutes preceding each programme a tuning signal is radiated consisting of two tones of different pitch, the one of lower pitch being on the A (left-hand) channel. This signal lasts for four minutes and is followed by one minute with no modulation. At the beginning of each programme there is a stereophonic announcement for setting-up purposes.

Test Tapes for South Africa

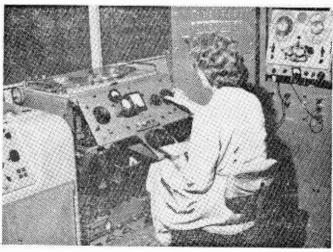
THE South African Broadcasting Corporation has placed orders with EMI Electronics Ltd. for test tapes for use in its broadcasting studios.

The test tapes comprise a sequence of pure tones over a very wide range of frequencies recorded at predetermined intervals. Such test tapes are recorded at the Hayes plant of EMI Electronics Ltd., using magnetic tape which has been carefully selected for uniformity along its entire length.

Tones from a special generator and their related prerecorded announcements, which give an audio indication of the tone to be played back, are recorded on magnetic tape using a specially modified and calibrated EMI studio tape recorder. All known corrections are made to allow for the differences between the replay head used during production and the head of a standard studio tape recorder.

The Largest Stabilised Power Supply

THE recent opening of the new Electronic Telephone Exchange at Highgate Wood by the Postmaster-General, Mr. Reginald Bevins, has brought to light some interesting information on the techniques of time-division multiplexing and



This illustration shows the type of specially modified recorders used by EMI to produce their test tapes, some of which have recently been ordered by the South African Broadcasting Corporation.

"memory" stores, etc., but the problems of supplying power were rather unusual.

The stabilised power requirements were presented to the Post Office by the five telephone companies of the joint committee whose individual members were responsible for separate

aspects of the exchange design. A.P.T. Electronic Industries Ltd. were invited to consider the overall requirements and to design and manufacture suitable

supplies. The result of this exercise was the production of four series-valve stabilised supplies which are probably the largest of their kind in the world. One unit which provides a mean current of 62A at +250V d.c., with peak currents up to 64A, utilises 180 valves type CV345 in parallel driven by a high-gain amplifier to cope with the variable aspect of the load in parallel with an unstabilised supply carrying the constant portion of the load current.

Carrier Frequency Stability Improvement

IN 1945 the BBC inaugurated high-precision frequency control of its 200kc/s transmission of the Light Programme The long-term from Droitwich. frequency stability, which was then within one part in 10°, has now been considerably improved and is maintained within five parts in 10°. The diurnal rate of frequency change of the 200kc/s carrier frequency is not greater than +1 part in 10¹⁰ and the resultant error will be corrected on the first Sunday in each starting calendar month 3rd February, 1963.

The availability of this trans-

mission will be increased to 201 hours each weekday during 1963 with the planned extension of the Light Programme transmission hours.

Equipment at the Audio Festival

AT this year's International Audio Festival and Fair to be held at the Hotel Russell, Russell Square, London, the EMI group of companies will display a full range of profes-sional tape recorders, a new stereo domestic tape recorder with general purpose loudspeaker enclosures, professional loud-speakers and Emitape.



A stabiliser rack for the 250V 62A stabilised power supply at Highgate Wood electronic telephone exchange.

The Audio Festival will continue from 18th to 21st April, when all this equipment will be on show to the public.

Radiotelephone Link for Lighthouses

TWO isolated lighthouses, 20 miles apart, whose only means of communication until recently has been a flashing lamp will in future use radiotelephones supplied by the Murphy Elec-tronics Division of the Rank The installation Organisation. will connect the lighthouses, situated off the south-east coast of Ceylon, with each other and with their mainland station at Kirinda.

The Murphy radiotelephones will be installed and ready for use by the end of March and are to be maintained and serviced by the company's agent in Ceylon.

Ultra-Sonic Aid for Blind Persons

A SONIC aid for blind persons, produced by Ultra Electronics Ltd. on the basis of a design by Dr. Leslie Kay, of the

Electrical Engineering Department of Birmingham University, has recently undergone a series of tests.

The aid consists of a transistorised transmitter-receiver which operates with a hand-held "torch", emitting an ultra-sonic beam of energy whose frequency varies with time. Any energy received back by the torch differs in frequency from that leaving it, at that instant, by an amount proportional to the time taken for the energy to travel out and be reflected back. Thus, by receiving the differing signals in an earphone, the blind person is able to judge the distance of an obstacle ahead of him.

After Dr. Kay had evolved a working system he approached the National Research Development Council and St. Dunstan's and NRDC requested tenders for ten of the devices for evaluation purposes. Ultra offered to produce the equipment free of charge and the offer was accepted. Work began on them in January last year and they were delivered in May, 1962.

A CATHODE RAY LEVEL INDICATOR

R. P. Hubbard

T is realised that this type of instrument has been described before in the P.W., but the "dead horse" is only flogged because of some unusual features that the device is believed to have.

Its three applications are: a visual signal tracer, an a.c. bridge null indicator and an absorption

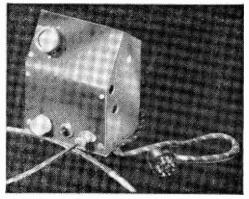
indicator for a grid-dip oscillator.

For this last application it is obvious that a good d.c. sensitivity is required. In fact, it proved quite easy to obtain maximum deflection with a change of only 1.5V. On the a.c. range, however, the sensitivity is much higher as another amplifier is switched in.

The cost of construction is very low; the valves being obtainable for about 10s. Nothing is particularly critical about the circuit, but if the described form is not followed, careful attention must be paid to the layout. This is because any stray hum can easily spoil the sensitivity, as also can any spurious oscillation caused by the anode circuit of the second valve coming near the input of the first valve.

The Circuit

The circuit is given in Fig. 1. The switch, S1, in the input circuit determines the mode of operation of the instrument; whether it is to be of low gain responding to a.c. and d.c., or of high gain responding to a.c. only. The a.c. signals are routed to V1, a high gain pentode amplifier. It may be noticed that the high tension supply to this

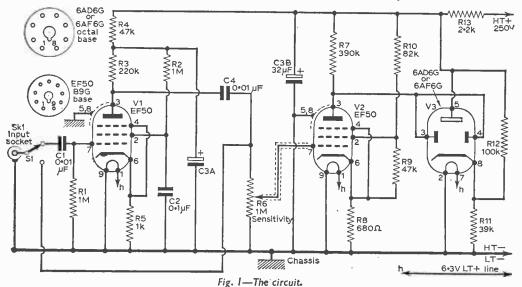


The author's prototype unit.

amplifier is very well smoothed and decoupled. This is to prevent any unwanted signals, e.g. hum, reaching V2. The cathode bias resistor, R5 in this stage, is left unbypassed so that negative feedback is produced which stabilises the amplifier.

The coupling capacitor, C4, must have negligible leakage or a potential will appear across R6 and as it is rotated the shadow angle on the display will change. The a.c.-d.c. and a.c. signal paths rejoin at the sensitivity control, R6, and the controlled signal is taken from the slider of the control to the grid of V2. V2 is in a special amplifier that produces an output of over 150V peak-to-peak. (It should be mentioned at this stage that the amplifier was designed only for high output with no consideration for distortionless output, as this is quite unnecessary.) The gain of this amplifier is over a hundred for maximum output, but is much more for small outputs.

By means of the resistance network, R8, R9, R10, the potentials on the screen grid and cathode are held steady at approximately 100V, and 1.5V respectively. In the quiescent condition the



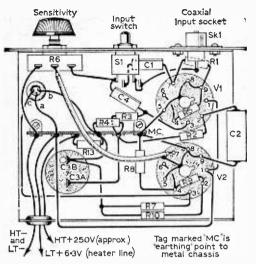


Fig. 2—The complete wiring diagram.

notential on the anode is about 50V. The anode is connected directly to the deflector plates of V3 which has its target connected to h.t. + and its athode held at about 100V above chassis optential. This is to fulfil the requirement that for change in shadow angle of 135°, the deflector lates should change from -50 to +75V when here is 150V at the target.

The components C3B and R13 were first neluded to isolate the instrument from a power upply common to other equipment, but in the interests of reducing hum level it would be advisble to retain them even if a separate power supply

vere to be used.

The power required to operate the instrument is

+75A at 6.3V and 5mA at 250V.

If it is so desired, other valves could be used, uch as EF91's instead of the EF50's An EM84 r EM85 could be used instead of 6AD6G or AF6G but R11 and R12 would probably have to

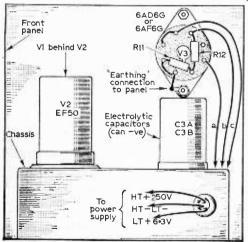


Fig. 3—Connections to the front panel.

COMPONENTS LIST Resistors: 82kΩ ½W 39kΩ ½W R1 $\mathsf{IM}\Omega$ **R5** IkΩ RIO R7 390kΩ R2 $\mathsf{IM}\Omega$ RII 680 O R3 $220k\Omega$ R8 R12 I00kΩ R4 $47k\Omega$ R9 47kΩ RI3 2.2kΩ R₆ $1M\Omega$ carbon potentiometer All resistors 4W, except RIO, RII. Tol. 10% or better for R8, R9, R10, R11, R12; others 20% Capacitors: Cl 0.01μF paper 250V C2 $0.1\mu F$ paper 250V C3A and B 32 + 32 μF elec. 350V C4 0.01μF paper 250V Valves: VI EF50 V3 6AD6G or 6AF6G V2 EF50 Miscellaneous: SI Single pole changeover switch Coaxial socket Skl

be changed. If either of these valves were used, the amplifier section grid should be connected to the cathode and the anode to h.t.+ through about $1\,\mathrm{M}\Omega$. In no circumstances, however, should the amplifier section be connected to the display section of the valve. It will be noted that the 6AD6G has no internal amplifier so this problem does not arise.

No difficulty should be found in the construction as no special techniques are used. The chassis and panel were made from 16s.w.g. aluminium sheet. Fortunately, an ex-government unit was available and it proved to be well suited for the

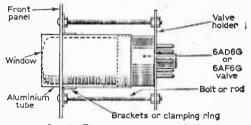


Fig. 4—The mounting details of V3.

purpose as the upper half sloped backwards. A sloping front panel is strongly recommended as it aids viewing considerably.

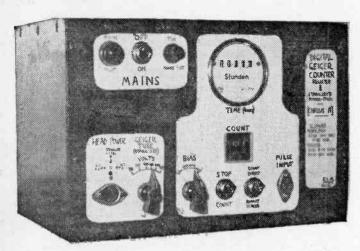
In the prototype instrument, the smoothing capacitor was of the twist-prong mounting type, but if the constructor has one of these and does not wish to cut the special holes, the capacitor can be mounted easily in a conventional mounting clip.

The housing for the display valve was made from an old halibut oil capsule container which had a hole cut in one end, reduced to the required length and bolted to the chassis together with the valve and valveholder (see Fig. 4).

It will be noticed that there is no provision for the detection of r.f. signals. This is because the instrument would almost invariably be used with a long coaxial cable or screened lead in the input, the capacitance of which would upset the working of high frequency circuits. It is therefore recommended that a suitable detector circuit be made up on the free end of the input lead from a semi-conductor diode.

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Geiger Counter Digital Register



incorporating Scaler and Power Pack

by E. Dexter

THIS ARTICLE DESCRIBES A DIGITAL REGISTER FOR OPERATING THE ADVANCED GEIGER HEAD DESCRIBED IN THE DECEMBER 1962 AND JANUARY 1963 ISSUES.

HE complete circuit is shown in Fig. 1. Around V1, a normal full wave rectifier, is a conventional h.t. supply circuit. A valve rectifier was here chosen because of the necessary high a.c. input voltage to compensate losses in the subsequent stabiliser, making it difficult to get suitable metal rectifier units of reasonable price and size capable of fitting into the small overall dimensions of the whole unit. V2, V3 and V4 and associated circuitry form a conventional electronic h.t. stabiliser.

V3 compares the voltage at the slider of VR1 with the reference voltage present at the neon V4, and amplifies any error detected. The amplified result is used to bias V2, the series-stabiliser valve, in such a sense as to correct the error. C5 serves to perform the same function for a.c., i.e. to remove remaining ripple and other disturbances from the output. The final output from V2 cathode is thus a very steady h.t. supply, whose voltage is virtually independent of input mains voltage fluctuations and output loading, within the rated output of about 25mA. The voltage is determined solely by V4 and the setting of VR1, and is arranged to be continuously variable from about 200 to 350V, by means of VR1.

The circuitry around V8 to V11 will be recognised as an incorporation of the already published simple digital counter circuit, with only some minor modifications to suit present purposes. The most important of these modifications is here that the output pulser V11, operating the digital relay, is given its own separate (unstabilised) h.t. supply from a tapping on the mains transformer and D1, R3, C3, C4. This is to prevent any interference with the many other circuits in this unit when the digital relay takes its heavy surges of

current on each count. Whilst this measure wa not needed in the simple digital counter alread published, its omission here causes primar interference with the new circuitry around V7, th digital scaler.

BINARY SCALER

This digital scaler serves the function of censoi ing the input pulses from the Geiger head, and no allowing everyone through to the counter, but onlexactly alternate ones, regardless of the statisticall random intervals between successive pulse characteristic of this whole field of work. V7 thu posesses a "Memory"; it can remember, for quite unlimited long time if necessary, whether let the last pulse through or not, and thus whethe it must let the next one through or not, regardles of how long it must wait for it, whether thousandth of a second or many hours. I "forgets" only if the whole unit is switched o in the meantime, of course! V6 is a pulse pre amplifier, operative only when the memory circu (binary scaler, V7) is in operation, to make certai that a sufficient amplitude reaches V7 for prope functioning under all circumstances.

It is seen that S3 enables the unit to be switche for direct feed of all pulses into the counter, or fc "divide-by-two" scaling via V7, at will. Specia switching arrangements insensitive to stray capacities have been devised, enabling a simple toggl switch to be used with full success.

NEGATIVE POWER SUPPLY

Finally, the power supply section contains ye another (negative) stabilised supply over D2, R12 C7, C8. This provides two separate stabilise

negative voltages: one of about 100-110V for bias operation on the digital counter section (from V5), and the other, using V5 and the power Zener diode D3, to give a supply of about -130-140V for the Geiger tube cathode feed. This voltage is somewhat higher than originally specified for the head, yet is perfectly satisfactory without any modification of the head whatsoever. The reason for this measure is as follows. The Digital Counter Section will operate well over an h.t. range of 210 to 340V, needing nothing but slight bias correction on VR2 for the various voltages, and even this is necessary only if the input pulse amplitude from certain head circuits is small.

The various samples of the specified Mullard MX124/01 tube and similar types have operating voltages lying between about 340 and 470V. The difference between this range and the counter range is seen to be around 130-140V, explaining why this voltage is then used for the Geiger tube cathode, thus allowing the Geiger tube anode to be fed from the same stabilised h.t. as the Digital Counter. However, this voltage is too high for counter bias input to VR2. as it would make adjustment of VR2 too harsh and critical. Thus the full negative voltage is supplied by the neon stabiliser V5 and the Zener diode stabiliser D3 in series, using only the correct portion for VR2.

Note carefully that the calibration to be placed on VR1 is to be such as to indicate the actual full Geiger tube voltage being applied to the head, i.e. the actual positive h.t. being produced plus the constant stabilised negative voltage. The h.t. value alone is of no interest. Calibration of VR1 is thus to be performed against a meter connected between the h.t. and bias pins of the Head Power Feed Socket, P1.

A self-starting synchronous clock unit is used for timing the counting period, this being switched simultaneously with the digital counter section h.t. (S2). It is important to use a self-starting synchronous clock-unit, preferably also with a digital time display instead of by means of hands on a dial (operation-hours timer for industrial machinery).

Those constructors well versed in metal and lathe work can easily make their own digital timer, using any cheaply available loose self-starting synchronous motor as sometimes advertised in these pages, driving a suitable counter such as a cyclometer or revolution counter through suitable gearing.

PROTECTIVE DEVICES

The electrical protection is simple, using just a mains primary fuse of 500mA or 1A (slow-blow) rating, certainly no higher rating. This gives normally adequate protection, provided one does not use a mains transformer of larger rating than here specified—particularly, one should not use an item with further (then unused) additional secondaries.

The type of transformer specified is a perfectly

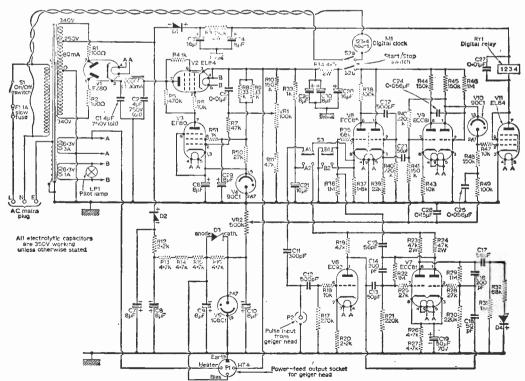


Fig. 1: The complete theoretical circuit of the digital register.

standard item, with 340-0-340 windings for a maximum of 60 to 80mA (350-0-350 will do, too). The windings must be tapped at 250-0-250V. Two heater windings are needed, one at 6:3V 3A for all valves except the EL84 (V2), which is run off a separate 6:3 1A winding also feeding the pilot lamp. The rectifier is fed from the main 3A heater winding with one side earthed, as it has a normal heater-to-cathode rating of 500V.

Only the EL84/V2 cannot tolerate this high heater to cathode voltage, and thus requires the separate heater supply, one side of which is

commoned to its cathode.

VENTILATION

It is extremely important to pay attention to proper ventilation in circuits of this type, because they must be capable of extremely long periods of non-stop operation—far more so than ordinary

wireless sets and amplifiers.

The present circuit contains eleven valves, yet uses a quite small compact design. It is thus clear that the use of any old layout in a closed cabinet is likely to promote the interior reaching the conditions of a small furnace after very few hours, giving early breakdown. Some simple thermal principles must therefore be understood and made they are of general applicability. The following facts are to be made use of:

- (a) A component does not reach a certain temperature as such, but a certain required excess temperature over its surroundings, in order to dissipate the wattage lost in it.
- (b) The exterior colour of the component influences the necessary excess temperature per

watt needed, all else being unchanged. The darker the colour, the smaller the necessary excess temperature per watt.

(c) The required excess temperature is greatly reduced if the air is allowed to circulate away

(convection).

(d) Where a component does not produce heat itself, but is close to other heat producers, it must ideally be polished bright, so as to reflect

heat rather than absorb it.

It follows at once that the use of asbestos within the cabinet can probably do more harm than good. It is best to line the cabinet top inside with a bright piece of sheet aluminium. Spacing this in a sloping fashion from the wood (see Fig. 4), it reflects heat and guides it easily out of a suitably generous ventilation slit at the back. Because it is brightly polished, it hardly heats up itself, even though powerful valves immediately below it may be belching heat up against it.

In conjunction with this very effective measure, a right and a wrong layout can make all the difference. The principal heat-generating components in the present circuit, V1, V2, V11 and the mains transformer, are mounted near the rear of the cabinet, so that a strong convection current cools them locally at the rear, without the heat ever getting into other parts of the cabinet.

Finally, whatever one may think aesthetically, a good jet-black external finish to the cabinet is highly desirable, as it keeps the exterior cool. Also, it is in fact the most "neutral" for sober laboratory apparatus anyway.

Note also the small clearance of the chassis either side from the inside cabinet sidewalls (Fig. 4). This is very important, to prevent sub-

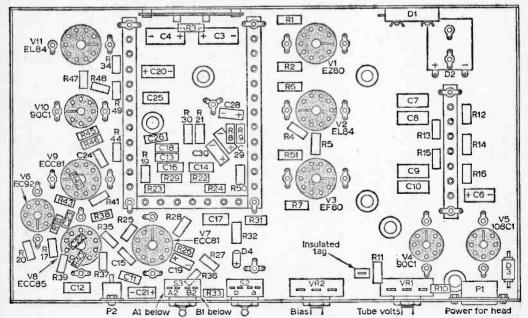


Fig. 2: The layout of components. The frame of chassis connection wires, with numerous cross-connections and earthing points, should be in bare tinned copper wire. Connecting wires on components are cut short at all flying connections.

LIST OF PARTS	C20 14 E de malaria 250V
1	C20 6μF electrolytic 350V C21 16μF electrolytic 350V
Resistors: RI 100Ω R27 $4.7k\Omega$	C22 500pF)
	C22 500pF Ceramic 500V
R2 100Ω R28 $27k\Omega$ R3 $2\cdot 2k\Omega$ 2W R29 $1M\Omega$	C24 0.056µF)
1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1	C25 0.056µF Paper 500V
$ \begin{array}{cccccccccccccccccccccccccccccccccccc$	C26 0·15µF
$R6 10k\Omega$ $R32 68k\Omega$	C27 0.01 uF
$R7 47k\Omega R33 1k\Omega$	C28) 0. F. J. J. 2501. (10
R8 33k Ω R34 4.7k Ω 2W	C28 \ 8μ F electrolytic 350V (if space, single
R9 33k Ω R35 68k Ω	C30 16µF in place of C28 plus C30)
RIO 150k Ω R36 IM Ω	Valves, Diodes:
RII $47k\Omega$ R37 $1.8k\Omega$	VI EZ80 Noval V7 ECC81 Noval
R12 $2.2k\Omega$ R38 $100k\Omega$	V2 EL84 Noval V8 ECC85 Noval
R13 $4.7k\Omega$ R39 $22k\Omega$	V3 EF80 Noval V9 ECC81 Noval
R14 $4.7k\Omega$ R40 $220k\Omega$	V4 90CI B7G VIO 90CI B7G
R15 4·7kΩ R41 150kΩ	V5 108C1 B7G VII EL84 Noval
R16 $4.7k\Omega$ R42 $220k\Omega$	V6 EC92 B7G
R 17 270k Ω R43 $10k\Omega$	DI Selenium E250C50 Rectifier
R18 $10k\Omega$ R44 $150k\Omega$	D2 Selenium E250C50 Rectifier
R19 $47k\Omega$ R45 $150k\Omega$	D3 Power Zener Diode, 33V 20mA (ZL33)
R20 $2.2k\Omega$ R46 IM Ω	D4 Fast Silicon Diode, 350V Inverse, 25mA,
R21 220k Ω R47 $10k\Omega$	10pF (S36)
R22 IM Ω R48 I50k Ω	Switches:
R23 47k Ω 2W R49 100k Ω R24 47k Ω 2W R50 27k Ω	SI I-pole ON/OFF \ \ Q.M.B. toggle
$\begin{array}{cccccccccccccccccccccccccccccccccccc$	S2 2-pole ON/OFF switches, 250/500V,
$\begin{array}{c ccccccccccccccccccccccccccccccccccc$	S3 2-pole/2-pole ON/ON) insulated toggles
VRI 100kO lin)	(If \$3 unobtainable, use 4-pole, 2-way rotary
VRI $100k\Omega$ lin VR2 $500k\Omega$ lin and 2 pointer knobs	wafer switch)
All carbon, I watt, ±10%, unless otherwis	e Miscellaneous
stated.	TI Mains transformer. Secondaries: 340-250-
Capacitors:	0-250-340V 80mA; 6·3V IA; 6·3V 3A
CI 4μF Oil-paper 750V	LI Smoothing choke, 15 Henry 1000 ohm
C2 4μF Oil-paper 750V	30mA (approx.)
C3 I6µF Electrolytic 350V	RYI Digital relay, approx. 1-2k (G.P.O. Tele-
C4 8µF Electrolytic 350V C5 0.01µF Paper 500V	phone-Call Counter)
C5 0·01μF Paper 500V C6)	MI SELF-STARTING synchronous motor driv-
C7	ing digital hours-counter (for 50c/s mains,
C8 ≥8µF electrolytic 350V	local voltage) FI Panel fuse, mains, IA slow
C9 C9	
C10 1	LPI Red pilot lamp for panel, 12volt 0-1-0-2A bulb (see text)
CII 300pF)	PI 4-pole/500V non-reversible panel-socket
C12 500pF	P2 Panel-mounting coaxial socket
C13 50pF	Chassis: Aluminium, 10 x 6 x 2in.
C14 200pF Ceramic, 500V	Main lead, plug. Connecting wire, tagstrip,
CI5 56pF	sleeving, bolts, etc.; Solder.
C16 200pF	Wood and screws for cabinet
C17 56pF C18 50pF	Aluminium plate for heat-deflection (see text)
C19 50µF electrolytic 70V	Valveholders: seven B9A and four B7G ceramic
Some electrolytic 70V	with skirt

chassis overheating. In this connection a spaced chain of resistors R12 to R16 was used instead of a single resistor of high wattage rating. This prevents undue localised subchassis heat-production.

These factors cannot be over emphasised, as once one has taken the trouble to produce such a unit as here described, one wants to concentrate on the interesting experiments possible with it, and not have these interrupted by frequent breakdowns. If the points here discussed are carefully attended to, and just that little bit extra spent on really good reliable parts in the crucial positions instead of saving a few pence by using any old junk, the unit described in this article will be found to give long and reliable service.

THE DIGITAL COUNTER

The principles of this circuit have already been discussed in detail in the article "A Digital Counter" by Mr. A. Cole, P.W. Feb.-April, 1962.

The same circuit has been incorporated here with little change. The separate h.t. feed for V11 has already been mentioned. V11 has also received a grid-stopper here. R47, necessary to cure some parasitic instability at first resulting with the different layout and conditions here adopted. It was also necessary to place a grid-stopper, R35, at pin 7 of V8 to cure initial further violent parasitics resulting from distributed inductances of the switch-leads on S3.

—continued on page 1094

OUR FREE GIFT

CALCULATOR

FOR PARALLEL RESISTORS AND SERIES CAPACITORS

by F. P. Rozee

HE arithmetical calculations involved in computing the equivalent value of resistors in parallel or capacitors in series, are sufficiently tedious to warrant the employment of some

mechanical means of computing.

The calculator enclosed with this month's issue of PRACTICAL WIRELESS has been specifically designed for this purpose. Compared with any other method of computation, even if it be by the use of a slide rule, this calculator can give the answer in a fraction of the time. Furthermore errors are most unlikely. It will be found that the accuracy is far better than the tolerance of practical components, in most cases closer than 2% can be read.

An inspection of the calculator shows that it consists of three scales, "A", "B" and "C", and two pointers. The left-hand pointer is used in association with scale "B", and the right-hand pointer with scale "A".

The answer is read off on scale "C" at the point of intersection.

Resistors in Parallel

The equivalent value of two resistors in parallel is found by setting one pointer to the value of RI on scale "A", the other pointer to the value of R2 on scale "B", the result Re is then read on scale "C" where the pointers cross.

Examples

R1	R2	Re
10	15	6
20	5	4
12	5	4
12	1	3

All of the above are easily read on scales "A" and "B". However for those combinations which cannot be accommodated on these scales, it is necessary to divide R1 and R2 by some convenient factor, to bring these values within the range of the scales. The reading obtained on scale "C

then multiplied by this same factor to give the correct answer.

For example, suppose R1 is 820, and R2 is 2,200. Dividing both of these values by 1,000 will bring these within the range of the scales. Therefore, set one pointer to 0.82 and the other to 2.2. This gives a reading of 0.6 on scale "C" which is multiplied by 1,000 to provide the equivalent value (Re) of 600.

One further example will make quite clear this method of extending the range of the calculator. R1 = 56, R2 = 36.

In this case it is convenient to divide by four

and the pointers are set as follows.

Scale "B" 14, Scale "A" 9. This gives a reading of 5.5 on scale "C" and Re is $4 \times 5.5 = 22$.

Adjusting Existing Values

It is sometimes required to bring an existing resistor in a circuit to a lower value. The calculator can be used then as follows: Assume the existing component to be $4.7k\Omega$ and that a value of $3k\Omega$ is required. Set the left-hand pointer to 4.7, then move the other pointer until the lines cross on 3 on scale "C", and read off on the left-hand scale, in this case 8.2. Therefore the value of the shunt resistor required is $8.2k\Omega$.

Capacitors in Series

The method of computing for capacitors in series is exactly the same as for resistors in parallel. The instructions will thus apply equally for resistors or capacitors. The terms R1, R2 and Re have been used for convenience, they can be considered where required as being C1, C2 and Ce.

Widely Differing Values

As most readers are aware, when one component is more than ten times the value of another, the higher value can usually be ignored as 10% or 20% tolerance components are normally used for radio and television work.

Determining the Decimal Position

Values are multiplied or divided by 10, 100, 1,000 etc. as required. There is no difficulty in determining the correct decimal position. The equivalent value of $120k\Omega$ and $56k\Omega$ for instance could not be $3.8k\Omega$ nor $380k\Omega$; it is obviously

Similarly a 0.2 µF and a 0.05 µF could only be 0.04 µF. The new value must lay somewhere between the value of the lower of the two components and half the value of the lower.

GEIGER COUNTER DIGITAL REGISTER

The value of R37 has also been reduced somewhat in comparison to the corresponding component in the original circuit—a measure by no means essential, yet giving somewhat increased sensitivity at the expense of a little greater interference from any spurious Geiger-kicks from the head (see below for further discussion of this point).

INPUT SWITCHING

The wiring around S3, the direct/scaler change-

over-switch, represents the major difference between

the present counter and the original circuit.

In the setting "direct", A1 and B1 are closed and A2. B2 open. Thus A1 feeds the input pulses to V8, pin 8 (cathode), via C11, the same as in the original publication, and every one is thus counted. B1 at the same time shorts the grid circuit, to stop interference from pulses also arriving capacitively from V7. V6 and V7 are dead in this position, because A2 is breaking their h.t. supply, although the heaters are on in "standby". The (dead) V6 further serves as a buffer in this position, to stop pulses also coming the wrong way.

CONTINUED NEXT MONTH

by C.M. and E.C.D.



conductors

TALKING POINTS ON CIRCUIT PRACTICE

No. 3-Audio Amplifiers

Continued from page 1030 of the March issue

E have now dealt with transistors under d.c. conditions and explained the necessity for them to be correctly set up to these conditions before they can be used for any purpose at all. Let us now consider them dynamically — as audio amplifiers.

There is no great problem involved in using transistors in audio-amplification configurations.

Any of the usual circuits can be tried.

Suppose the circuit Fig. I to be intended to amplify a small signal at r.f., imposing a variation of a couple of microamperes or even less on the base. With a gain of 50 in the transistor this will involve a swing of $2 \times 50 \mu A$ in the collector= $100 \mu A$. A standing collector current of ImA, with a suitable load, would accept this without bottoming the transistor on one hand or cutting it off on the other.

Suppose now that the stage is intended to be the ultimate or penultimate of an audio amplifier. The base input now will not vary in the order of microamperes but in the order of milliamperes. A change of say 10mA in the base will be 10×50 in the collector= $500=\frac{1}{2}A$. We are obviously not going to accommodate this in a standing current of 1mA. Or are we? In order to answer this, we must consider how the base input is to be applied, not merely how large it is.

For the moment, for the sake of clarity, we are ignoring the effect of the load resistor in the

Fig. 1: Common-emitter amplifier. Fig. 2: Need for adequate collector lq.

collector, but this also will limit the capacity of the transistor of course because apart from accommodating the current swing the output circuit must not drop so many volts over the load that the voltage limits are exceeded, either.

Now in the average case with the base isolated from its source of drive by a capacitor, the potential on the base will be that at the junction of the potential divider R1, R2 and the applied a.c., assuming a sine wave, will appear upon it as Fig. 2(a), moving the base positively on one half

bias on the other.

In an audio amplifier the wave will be in fact d.c. frequency modulated. But in this instant we will assume that it shall appear to the base as a.c. Assuming this we can draw some conclusions.

of the wave, negatively with respect to its standing

CURRENT SWING

The corresponding change in collector current will be an increment in the standing current when the base moves negatively and a decrement in the standing current when the base moves positively. Assuming a standing collector current of ImA, this can certainly rise by 50mA or what-have-you when the base moves negatively (provided the transistor is capable of handling 50mA peak). But since a reduction of ImA will mean no collector current at all it equally certainly cannot fall by 50mA when the base moves positively. In fact the transistor will cut off on the positive half of the drive and will amplify only one half of the input—which might be all right if we wanted rectification but is all wrong when we want linear amplification.

Quite obviously then the standing current in the collector will have to be at least 50mA in order to accommodate a swing of 50 above this and

50 below it.

Consider now the base of the transistor driven from a diode, Fig. 3(a). Again we set the standing collector at 1mA. Suppose current the diode to be inserted negativewise-that is, so that it passes only negative current to the base. sine wave entering the diode is as Fig. 3(b). Leaving the diode the wave is as Fig. 3(c). Now the base moves wholly negatively on its standing bias, inducing an increase in collector current varying according to the modulation as shown in Fig. 3(d). There is no positive move on the base and therefore no reduction of collector current. If base moves 5mA negatively on its standing potentials, at a gain of 50 the collector

will increase 250mA above its standing or quiescent value but will never drop below it. In this case obviously we can safely run the transistor on a quiescent collector current of only 1mA since the variation due to signal drive will be wholly incre-

mental-Fig. 3(d).

Now reverse the diode and connect it positive-wise so that it passes only positive current to the base. Here the signals on the base will be wholly the positive half of the wave, Fig. 3(e); the collector current changes will be wholly decremental; the collector current will try to move less than its quiescent value to the tune of 250mA downwards (on peak signal) and the transistor will cut off, Fig. 3(f). The result (and this occurs often enough) will be "no signals". Raise the standing collector current to a value of some 250 or 275mA quiescent, however, so that a reduction of 250 can be accommodated without cutting off the transistor and once again everything is jake.

IMPORTANCE OF PHASE

Now let us state the rule—namely, that not only the size of the incoming signal will have to be considered but also its phasing, whether wholly negativewise, wholly positivewise or effectively a.c. If you apply a positive-going signal to the base of a transistor already biased near to cut-off, and the signal is of any sort of amplitude, the transistor will cut off. If you apply a negative-going signal to a transistor already biased so that its standing current is near the maximum either according to published data (when an increment will destroy it) or according to its load so that any increase will cause all the available volts to be dropped, so bottoming the transistor, the result will be no signals.

A wholly negative-going input allows the transistor to be worked at low values of collector quiescent current, a wholly positive-going signal requires it to be worked at a high standing collector current; an a.c. input requires it to be worked at midpoint approximately on its output characteristic so as to accommodate both increment and decrement of the standing Icq.

These considerations do not need to worry us with small signals but in audio amplifiers where the currents and voltages can be considerable it is different. There is a misconception abroad that transistors cannot be used for large currents. Nothing is more mistaken. We have the GEX544, for instance, capable of charging your car battery to the tune of 5A and occupying no more space than a half-crown piece. Normal audio output stages may carry a current of anything from 100mA for the OC81 up to several amperes according to the transistors used; 20W outputs for public address systems can be achieved.

Perhaps we had better get out of possible trouble at this point by introducing Fig. 4 to explain that a wholly positive-going or a wholly negative-going signal on the base does not in practice modulate the base wholly upwards or below its standing bias,



Fig. 4: Shift of standing bias due to input signal.

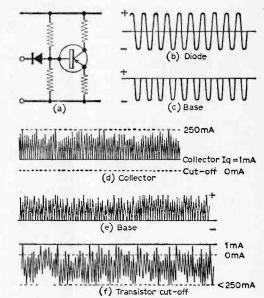


Fig. 3 (a), (b), (c) and (d): Negative-going input; (e) and (f): Positive-going input.

though for practical purposes it is usually enough to consider it so. In fact the standing bias on the base is increased or decreased to a new value by the addition (electrical) of the mean of the applied signal—the figure should make this clear enough—and the base moves about this new value. The standing collector current will thus increase or decrease on signal to a new value, moving with the frequency modulation around this; it may need to be calculated or not according to the size of the signals expected to be handled. If we allow ourselves a sufficient margin so that the collector current will never vary sufficiently to be near cut-off or bottoming we can ignore this factor.

But what we must remember in transistor technique is that the *phasing* of the incoming signal

may be important.

PRACTICAL AMPLIFIER CIRCUITS

Since transistors are normally battery operated it is obvious that push-pull circuits worked in Class B will normally be preferred in output stages on account of their saving in battery despite that they compare unfavourably with Class A where fidelity and hi-fi is concerned. A Class B output stage can give five times the output that one transistor would give alone or, put another way, the total dissipation of the two transistors in Class B can be five times that of either, thus enabling an output of 1W (from two OC81s, for instance, paired in Class B) to be achieved without either transistor exceeding 200mW at an efficiency of 80%. (Class A gives only 50% efficiency.)

The principle of Class B operation is that both

The principle of Class B operation is that both halves of the stage are biased to cut-off, thus drawing no current under no-signal conditions.

Considering a sinewave input, if we apply the negative half of the wave to transistor A (Fig. 5) the collector current will vary according to the



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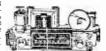
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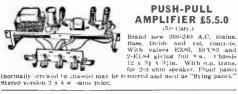
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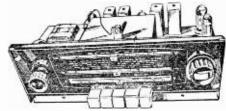
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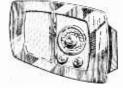


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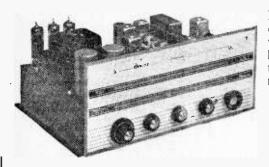
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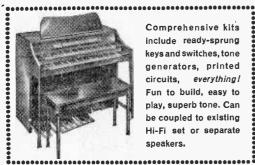
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modulation incrementally from 0V; the positive half of the wave will move the transistor into cutoff and will not be reproduced. If we can now apply the positive half of the wave to transistor B in such a manner that to transistor B it looks negative, transistor B will handle it while transistor A remains inoperative. This is achieved by a phase-splitter. It is often a centre-tapped transformer, but to understand the process consider the splitload stage, Fig. 6.

Here the collector load is half in the collector and half in the emitter and we have chosen 1k\Omega for each. When the transistor is driven on the base the collector current varies about its quiescent value in the normal manner. Assuming a standing value of 1mA and a line voltage of -9 under quiescent conditions the collector is at -8V and the emitter at -1V. An increase in current will cause the collector to become more positive, say an increase of 0.5mA, then the collector load drops another 0.5V and the collector is at 7.5V, while the emitter moves from -1V to -1.5V. Thus as the collector moves positively the emitter moves negatively.

Suppose we connect the collector to the base of transistor A (Fig. 7) and the emitter to transistor B (same figure). Both these transistors are biased

to cut-off under standing conditions. Neither is conducting. As the collector moves positively transistor A base moves positively and transistor A moves further into cut-off. But the same instant the current in the collector of the phasesplitter is moving the emitter negatively; this, connected to transistor B, moves the base of transistor B negatively and transistor B moves cut-off of out amplifies.

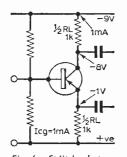


Fig. 6: Split-load stage.

When the current in the phase-splitter is moving decrementally on the positive half of its input the collector is moving negatively. This applied to transistor A brings it out of cut-off and into operation, while at the same instant the emitter of the phase-splitter is moving positively so that transistor B now moves *into* cut-off and becomes inoperative.

So each half of the Class B stage deals with one half of the input wave only.

The comparative transformer phase-splitter circuit is shown in Fig. 8. With the secondary centre tap earthed, when one end of the secondary is moving positively the opposite end will be moving negatively, and vice versa, so our conditions for Class B are fulfilled.

MATCHED PAIRS

The two output transistors must be matched. If the alpha (i.e., gain) of one is more than that of the other then one half of the input wave will receive more amplification than the other with consequent distortion. If response to frequency of the two transistors is not the same then some frequencies will receive more amplification in one

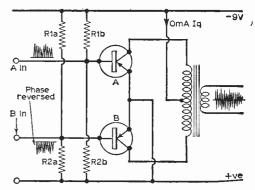


Fig. 5: Class B operation: both transistors biased to cut-off.

than they will in the other, or the cut-off frequency may be different and one may not reproduce at all frequencies which the other is reproducing. Transistors are sold in matched pairs to safeguard against this.

With transistors a phenomenon occurs at the moment when the two transistors are changing over which can cause considerable distortion. In order to get over this transistors in Class B are not run at quiescent cut-off; a small forward bias is given to each base allowing each to draw a small current under no-signal conditions. With R1 in each case consisting of a potentiometer the standing bias on each base can be varied within fine limits until the amount of standing current in each transistor is so adjusted that the minimum distortion results.

The circuit shown, Fig. 9, though quite theoretical, has been built and is capable of giving a perfect response at sufficient output to fill a small room and it is quite excellent to experiment with. It will NOT work from a radio receiver because the gain is insufficient to enable it to amplify the small signals from such a source to a sufficient extent. The actual gain of this circuit is round about 30 and we need at least 100 for practical purposes. The additional gain would normally be achieved by having a further "driver" stage either between

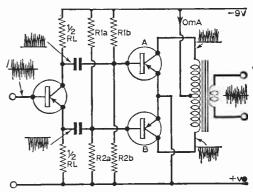


Fig. 7: Phase-splitter driving two output transistors.

the phase-splitter and the output or in front of the phase-splitter. The push-pull driver would be governed by exactly similar considerations to those we have discussed for the output stage except that since it will be handling smaller signals the standing collector currents will be chosen to have different values; the various resistances and loads can be higher as smaller values of current can be used.

SPLIT-LOAD PHASE-SPLITTER

But first let us examine the split-load phase-splitter again for a moment. To begin with it is obvious that with half the load in the collector and half the load in the emitter, each being applied to its own following transistor, the possible gain of this circuit must be considerably less than would be possible with the entire load in the collector. Transformer phase-splitting is, therefore, normally used, even though transformer coupling introduces possibilities of positive feedback and other forms of instability where maximum gain is required.

This transistor phase-splitter, however, is an excellent example of the importance of phase of

input in transistor work.

Consider a standing current of 1mA through load A and load B, each of $1k\Omega$ with a line voltage of -9. Collector stands at -8 and emitter stands at -1. Consider now the stage driven from a diode connected positivewise. The collector current is varied decrementally. A variation of input of 100mA at a gain of 50 produces a change of 5mA in the collector circuit decrementally. You cannot reduce the collector current by 5mA when you have only 1mA to start with, so the result is "no signals". The transistor moves into cut-off.

Reverse the diode, connecting it negativewise, and you now have an incremental change in collector current from ImA standing (leaving out the change in the standing bias for the moment) to 6mA. The emitter moves from -1V to -6V (the $1k\Omega$ load dropping 6V at 6mA); at the same time the collector moves from -8V to -3V. Once again we have "no signals" because we are left with no volts across the transistor at all, the transistor, in fact, is bottomed at peak signals.

If we are to leave on peak signals at least 1V across the transistor so that it does not bottom on peak signal we are left with only 8V of the possible 9V to play with. All the time in

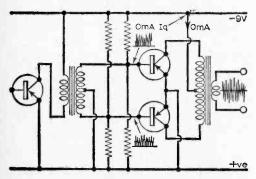


Fig. 8: Transformer phase-splitter.

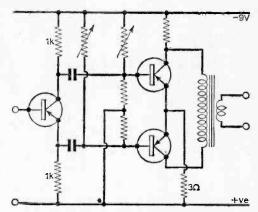


Fig. 9: An experimental circuit.

transistor work one is up against this question of

limited supply volts.

Each half of the load must, therefore, not drop more than 4V if 1V is to be left across collector/emitter junction on peak signal. $1k\Omega$ will drop 4V at 4mA, so this is the maximum collector current we can allow ourselves on peak signal. With a transistor gain of 50 this means that our peak input must not exceed $4/50\text{mA} = 0.08\text{mA} = 80\mu\text{A}$.

Now consider the phasing of the input. Suppose it is all negative from a diode connected negative-wise. The collector current therefore increases. But we have ImA standing current, dropping already IV over each half of the load; we can therefore accept only an increase of 3mA before we are dropping our 4V across each half. Suppose the diode is connected positivewise, causing a decrease in collector current; we can accept only ImA decrease before we reach the stage of no current at all—i.e., cut-off.

Suppose there is no diode and the input is sinewave a.c. The output will distort on the positive side as soon as ImA is reached, for there the transistor will cut off while being able to take 3mA on the negative half of the wave before squaring commences as the transistor starts to bottom.

Assuming sinewave a.c. then, we will have to work the transistor at the midpoint with regard to both loads. A value of 2mA standing current will place the emitter at -2V and the collector at -7V. The collector can now move 2V positively to 5V and 2V negatively to 9V, while the emitter can move 2V negatively to -4V and 2V positively to +6V.

Alternatively, assuming a diode and therefore a unidirectional input, if the diode is connected negativewise then the standing bias must be such that the transistor quiescent collector current is almost nil if we are to accommodate the maximum signal amplitude; conversely, if the diode be connected positivewise then the transistor must be biased so as to take nearly the maximum collector current (short of bottoming) if it is to accept the maximum decrement before it cuts off altogether.

SERIES CONTINUED NEXT MONTH

By A. Cole

Quality Amplifier

Continued from page 1021 of the March issue

THE TUNER

It also avoids the extreme distortion experienced

HIS tuner is of a relatively advanced design, and should only be attempted by the experienced constructor. Three i.f. stages are used on f.m. giving unusually high gain. Very high sensitivity and selectivity is obtained on the a.m. channels, one longwave (Light Programme) and three mediumwave (Home, Third, Luxemburg) pre-tuned channels being selectable by a second switch (S1). These positions have individual coils, so the cores may be re-set for any alternative stations.

The high sensitivity and selectivity is obtained by using a high-gain r.f. stage ahead of the frequency changer. A.G.C. operates on three stages and is delayed by about a volt at R38; the action is thus very effective for reception of Luxemburg.

The f.m. tuning head is a *Heathkit* model FMT-4U. This uses an ECC85 as r.f. amplifier and frequency changer. In the circuit diagram only components to be inserted new inside this unit are given reference numbering.

Experienced constructors could attempt to build the r.f. head themselves, but it is very critical. The author initially constructed two home-built designs of this head, both of which worked well, but with sensitivity well below that of the Heathkit Unit. It is extremely difficult to get optimum home-built coils for this unit.

Therefore it was finally decided to use a commercial head, to guarantee success to all constructors. No other part of this design should

offer particular difficulty.

The v.h.f. head must, however, be modified for application of Automatic Frequency Control (a.f.c.). While this would be essential for a homebuilt head, to prevent oscillator drift, this trouble does not arise with the Heathkit unit because it employs accurately matched temperature-coefficients on the relevant capacitors. Its purpose in the present design is to simplify the tuning, so that only a knob directly on the tuning-spindle suffices, slow-motion drives and dials being unnecessary. This permits a clear, simple and "open" panel design characteristic of switched tuners.

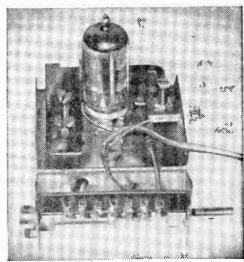
The action of the a.f.c. is that, once a station is even partially tuned in, it automatically slips into exact tuning and locks there, even for the moderate displacements of the tuning control. This gives easy tuning while maintaining full high selectivity.

when an f.m. tuner is set slightly off a station.

Quality deteriorates with mistuning much more severely on f.m. than on a.m., so that spot-on tuning is required. The a.f.c. circuitry in the present design incorporates a capacity diode, type BA110.

The Capacity Diode

A capacity diode is a semi-conductor device in the form of a small diode operated with a d.c. polarising voltage in the non-conducting direction, i.e. cathode positive to anode. The higher this polarising voltage, the smaller is the effective



The Heathkit f.m. tuner head, used in the tuner.

capacity presented by this diode. The circuit to which the diode is connected thus "sees" merely the equivalent capacity, which can be varied over a large range by variation of the polarising voltage. It is, of course, essential to use "normal" blocking capacitors where necessary to prevent the polarising voltage influencing the other circuitry, such as C1 in the modified r.f. head.

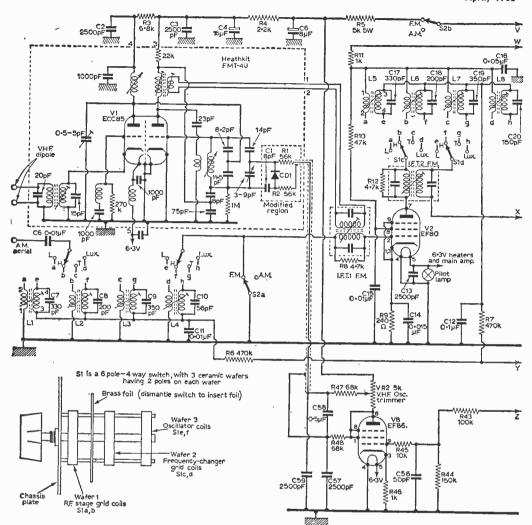


Fig. 9a: The r.f. and a.f.c. stages of the circuit.

The added resistors R1 and R2 serve to prevent loading of the oscillator through the a.f.c.' d.c.-control line. The d.c polarising voltage is applied to the far end of these resistors, through a thin screened cable, which can be taken out through the adjusting hole of the i.f. coil. As the screening of this cable is at some h.t. potential, do not connect it to chassis, and use a cable with final external insulation (microphone cable).

In wiring the a.f.c. components in the r.f. head take care to prevent mutual shorting or shorting to the re-assembled outer aluminium casing subsequently. The head is opened by prising off the two end caps, removing the holding screws at the sides, and then bending the outer aluminium casing apart until the internal chassis-unit can be slipped out. Assemble in the reverse order.

Fig. 11 gives details of the BA110 capacity diode, showing the relationship between effective

capacity and applied polarising voltage. It is seen that a polarising voltage of some 4V is needed to give about 8pF effective capacity, which together with CI restores the original capacity of about 4pF of the removed original fixed capacitor.

The polarising voltage is adjusted by VR2 (in the anode circuit of V8) which thus functions as v.h.f. oscillator trimmer. It should be set about a third to half rotation from the anode end. C1 (if necessary) and the oscillator core should then be adjusted during aligning to restore correct coverage (88 to 108Mc/s); the r.f. trimmer may also need re-peaking.

Ratio Detector and A.F.C.

V6 is a conventional ratio detector. At the centre frequency of the passband, voltages induced in the IFT5 secondary are such that the diodes

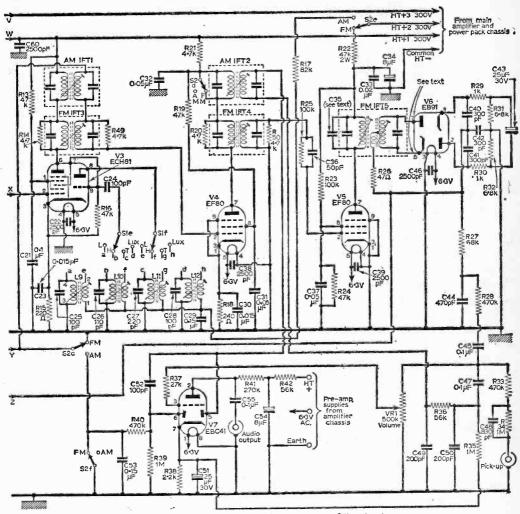


Fig. 9b: The i.f., detector and audio stages of the circuit.

receive equal signals, which appear respectively (rectified) across C40 and C41, and in such polarity

that their sum appears across C43.

If the signal frequency deviates from the centre, the phasing in the IFT5 coils is such that the diodes receive different signals and C40/C41 carry different rectified voltages. However, provided that the amplitude does not change during the frequency excursions, i.e. provided we have pure f.m., the sum of the voltages across C40 and C41 (across C43) remains constant over a wide band. If the alignment is not correct, however, distortion is heavy.

If either a pure a.m. signal is present, or unwanted a.m. together with the wanted f.m., the voltages on C40 and C41 will attempt to follow the rhythm of the amplitude modulation. But they are hindered by the extremely large capacity of C43, which cannot follow so quickly. Thus C43 imposes

heavy and variable damping on the circuits of IFT5, through the diodes, shorting out the modulated portion of any a.m. signals. R29 to R32 give this a.m. damping optimum time constant and characteristics.

Although the ratio detector is inherently insensitive to a.m. and does not, basically, require a previous limiter stage, its a.m. rejection is not perfect, and a limiter is still desirable. The final i.f. amplifier V5 is built as a leaky-grid rectifier limiter operating with starved screen voltage to

give anode bottoming.

Negative excursions of amplitude are clipped on the grid-base due to the rectified signal bias developed across R25 and C36, and positive excursions are clipped by anode bottoming. The output signal is thus, at the anode, free of amplitude modulation. A point to watch carefully when using this kind of limiter is that it operates as

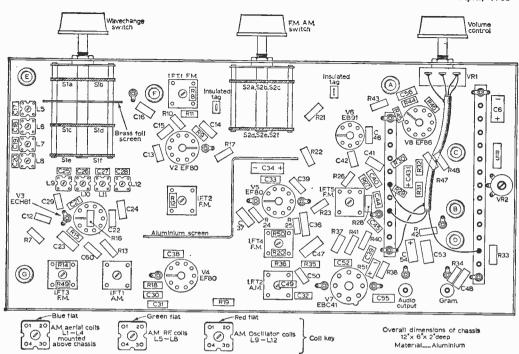
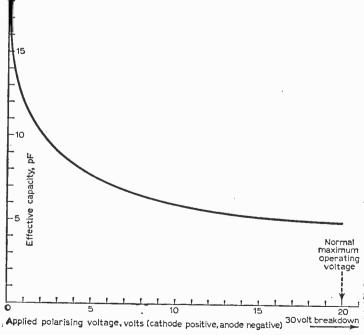


Fig. 10 (above): The layout of components.

Fig. 11 (below): How variation of polarising voltage affects the capacity.



leaky-grid detector for any a.m. present, the a.m. which it removes from the i.f. waveform appearing at the anode as audio.

Furthermore, if the r.f. head is tuned off to the signal flank the f.m. signal will also deliver an audio output at V5 anode by virtue of "flank detection". If these audio components are allowed to develop, capacitive coupling through IFT5 and out through R26, R27 into the main audio amplifier chain can be appreciable.

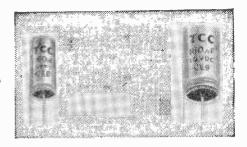
Such "stray" audio can reach amplitudes up to 5 or 10% of the wanted signal, and is often extremely distorted. The net result would be an enormous increase of distortion in the audio output. To remove all trace of this effect, C34 is included to short-circuit the anode load (R22) for audio frequency. The small parallel capacitor C33 is still needed to give i.f. decoupling, as electrolytics alone can have far too high an impedance at 10.7Mc/s. -- CONTINUED ON PAGE 1107



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T.C.C. TYPE	CASE SIZE IN INCHES			MAXIMUM D.C. WKG. VOLTAGES AND CAPACITANCE (μF)			ND			
(176	D	L	С	3V.	6V.	IOV.	15V.	25V.	50 V .	
CE.8	‡	3 4	0.14	100	80	60	40	25	8	
CE.9	1	34	0.2	250	200	160	100	60	20	

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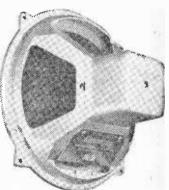
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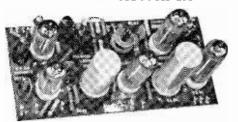
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The effectiveness of suppression by C34 should be checked by withdrawing V6 from its socket, when no signals should remain audible at any tuning setting. If distorted audio signals exceeding 1% of the normal output amplitude are heard, C34 must be increased in value.

If no signals at all are heard from the finished tuner until C34 is disconnected, and then only weak and distorted signals which remain when V6 is pulled out of its socket, check the valve base connections of V6 as a mistake here is very

common.

Audio Output

C43 is balanced to earth by means of the two load resistors R31, R32, the junction of which cannot follow the voltage fluctuations with frequency modulation present at the junction of C40, C41, because of the shunting of C43. Consequently the fluctuations appear across C42 as corresponding detected audio voltages and are fed via R27 to the a.f. stages, de-emphasis being provided by R27, C44.

The A.F.C. Signal

If the i.f. signal should be displaced from the centre of the i.f. passband, due to inaccurate setting of the tuning control on the r.f. head, then the potential of the junction of C40 and C41 is permanently displaced from the earthed junction of R31, R32. The polarity is according to the sense of the tuning error.

The error signal is d.c. coupled through R43 to the grid of V8, functioning as a d.c. amplifier and automatically adding the polarising voltage by virtue of standing anode current drop in VR2. The amplified error signal output from VR2 is thus of a form suitable for application to the capacity diode in the r.f. head, to correct the original detuning giving rise to the error signal.

For the a.f.c. function, V6 functions as a true d.c. discriminator, operating on the tuning of IFT5 as reference standard. It is thus essential that the i.f. transformers in the v.h.f. chain, especially IFT5, are properly aligned. Once the i.f. amplifier begins to "see" the sidebands of an approaching v.h.f. station, it generates a control voltage for the local oscillator to lock the signal immediately on to the centre of the passband and hold it there even after moderate temperature drift.

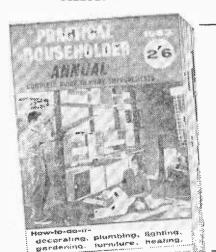
The gain of V8 is not high as the levels at the ratio detector are already ample. Its main purpose is to achieve a simple and stable insertion of the polarising voltage for the capacity diode without back reaction on the ratio detector. Another arrangement was tried, using a high-gain double-triode balanced d.c. amplifier with Zener diode stabilisation. This gave such powerful a.f.c. that once a station was locked in, one could not get rid of it again right round the dial, as the a.f.c. control could drag the oscillator round the entire tuning range. The aerial had to be removed momentarily to get rid of the station, and then get another (pure chance which one then, too!).

TO BE CONTINUED



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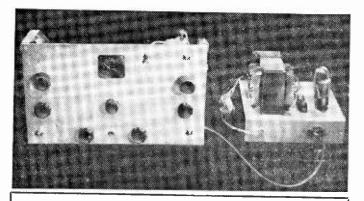
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FOUR VALVE TRANSMITTER

For 3.5 and 7Mc/s

by S. F. Appleyard, G3PND







The transmitter described in this article was built before the author obtained his transmitting licence in order to learn more on the subject of transmitters before sitting for the Radio Amateur Examination. The knowledge derived from designing and building the transmitter proved invaluable not only for the R.A.E. but several other radio examinations taken since. If the transmitter is built by someone not at present licensed, they are reminded that they must not put the transmitter on the air even for testing purposes, but there is nothing to stop anyone who is licensed testing it for them.

HE transmitter was intended to be simple and straightforward, operating on 3.5 and 7Mc/s c.w. only. It uses four valves: EF91, EF80, 6V6 and 807; and runs 25W to the final stage. All the

parts were out of the junk box except the chassis and front plate which were purchased for approximately £1. As most of the components were already at hand the values of some are not as accurate as might be but nevertheless the transmitter worked extremely well.

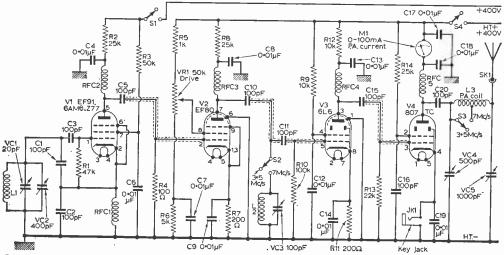


Fig. 1: The circuit diagram of the four-valve transmitter. A suitable power pack for this unit is shown in Fig. 4.

THE CIRCUIT

Now taking the transmitter stage by stage, the oscillator (V1) uses a pentode in a Colpits circuit. Several circuits were tried and this arrangement was chosen as it did not employ a tapped coil and proved reasonably stable. The frequency of oscillation depends upon the values of L and C

where $C=VC2+(\frac{1}{C1}+\frac{1}{C2})$. The values of C1

and C2 can be varied to alter the amount of feedback, but it was found to be best when both values while C5 acts as a low impedance to r.f. but blocks d.c. C5 also provides class C bias for V2 in conjunction with R4. Bias for this stage is also provided by the cathode resistor R5. When the second stage is used as a harmonic generator (frequency doubler) the tuned circuit L2-VC3 is switched in by S2. This tuned circuit operates on a frequency 2f, which is 7Mc/s.

DOUBLER AND BUFFER

The valve used for this stage is an r.f. pentode again, this time an EF80—but another EF91 could

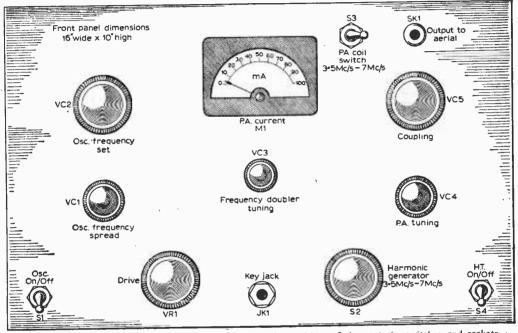


Fig. 2: Front panel layout of the transmitter showing the positions of the controls, switches and sockets.

were equal. The oscillator provides its own bias, since the valve runs into grid current and charges up C3 which leaks off through R1 during the negative half cycles and holds the grid at a negative potential. Thus if the oscillations were to stop, the cathode current would rise to an extremely high value as the valve would become unbiased.

The variable capacitor VC2 in the tuned L/C circuit of the v.f.o. is 400pF and this was paralleled by a 20pF capacitor VC1 which was used for final adjustment when netting. But this can be dispensed with if a slow motion drive is used in conjunction

with the 400pF capacitor.

The coil L1 was wound to resonate with the capacitor on 3.5Mc/s, which is the fundamental frequency of the transmitter. When the transmitter is required to operate on this frequency the signal is fed straight through two untuned amplifiers to the p.a., but when operation on 7Mc/s is desired the second stage (V2) acts as a frequency doubler. The radio frequency choke RFC2 in the oscil-

lator acts as a high impedance load to valve VI,

be used providing some modifications were made. The circuitry with this stage, as with the next, is very straightforward but one point worth mentioning is that at this stage the drive is controlled by VR1. This control varies the h.t. applied to the screen of V2 and thus varies the anode current through the valve and hence the gain.

C9 bypasses the cathode resistor and thus prevents any negative feedback which would considerably reduce the stage gain, while the capacitors C5, C8 etc. decouple the h.t., preventing positive feedback and hence instability. The radio frequency choke RFC3 acts as a high impedance load while offering a very low d.c. resistance.

The output from this stage is taken to V3 which always acts as an untuned amplifier regardless as to whether operation is on 3.5 or 7Mc/s. The valve used originally was a 6V6 but it has since been replaced by a 6L6 but not a lot of difference has been noted. During construction at this stage the transmitter was put on the air using a lashed-up π tuning circuit, and with the assistance of a friend

(a licensed operator), several QSO's were made on 7Mc/s, with good reports.

POWER AMPLIFIER

The output from this stage is fed into the power amplifier and the valve used here is the well known 807. Keying of the transmitter is effected at this stage by the breaking and making of the cathode lead. It can be seen that the only means of bias for this valve is that developed across the grid leak resistor R13—there being no cathode resistor; so the key should not be pressed without the oscillator switched on, or the current flowing in V4 might damage the valve.

In the anode lead of the p.a. is a meter MI which should have a full scale deflection of 100mA. Each side of the meter is decoupled to earth as the meter leads are fairly long. The two decoupling capacitors C17 and C18 should have their live ends connected as near to the meter terminals as possible. The radio frequency choke RFC5, here again offers a high impedance load to the 807 valve while the capacitor C20 offers a low reactance to the radio frequency signals.

The aerial tuning circuit is the widely used π arrangement. VC4 is the tuning capacitor and VC5 is the coupling capacitor. Directions on how to load up the transmitter are given later.

Now the outlines of the transmitter have been given it is clear that it is simple and straight forward, which is what was intended. The whole transmitter is supplied from one power-pack (see Fig. 4) which supplies 400V at 180mA. V5 is an indirectly heated full wave rectifier type GZ33.

CONSTRUCTION

The chassis measures 16in. x 10in. x 2in. with a front panel 16in. x 10in. L-strips are taken from two top corners of the front panel to the two back corners of the chassis, to hold the front plate rigid.

The layout of components is not too critical as long as the p.a. is at the opposite end of the chassis to the oscillator. The oscillator coil is completely enclosed in a screened box and all oscillator components should be kept away from resistors, as the heat generated by the latter might cause some frequency drift. Components should be securely mounted and all wiring rigid to prevent frequency drift. All leads should be kept short and those carrying r.f. should be screened.

The layout of the valves and tuning capacitors is shown in Fig. 3. The p.a. valve must be screened. In the original, a cocoa tin was used with the lid taken off and the bottom cut out, but the screening can be dispensed with if the valve base is sunk into the chassis about 1½in. so that the electrode leads are below chassis level and are thus screened.

Smaller components were mounter on tag-boards and kept close to their respective valve bases. Power supplies are fed into the transmitter by a 4-core cable, the free end being terminated in a 4-pin plug which fits into the appropriate socket in the power unit.

OPERATION

After the transmitter has been connected to the power-pack and the latter connected to the mains supply, the oscillator h.t. switch S1 should be made

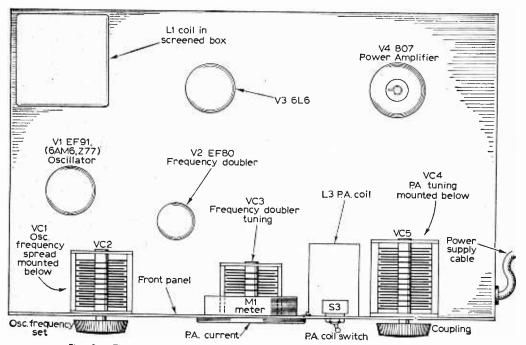


Fig. 3: This is a top-of-chassis layout showing the positions of the major components.

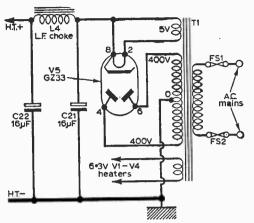


Fig. 4: This simple power pack provides 400V at 180mA and 6.3V a.c. to power the transmitter.

and then the oscillator tuned to the required frequency. Switches S2 and S4 should be set to the required band (3.5 or 7Mc/s) and the drive control set for maximum drive.

The transmitter is now ready for loading up to the aerial which should be already connected. Close switch S4 and press the key. There will now be a reading on the meter and if the output of the transmitter is to be on 7Mc/s the capacitor VC3 should be adjusted to give minimum reading on the meter.

The coupling capacitor VC5 should be originally set for maximum capacitance, i.e. plates completely intermeshed. The tuning capacitor VC4 should be tuned for a dip in the meter M1, this indicating the resonant point. The coupling capacitor VC5 should now be slowly turned until the p.a. current rises until it reaches 60mA, now retuning VC4 for another dip and again increasing the coupling until the p.a. current reads 60mA and finally finish up by retuning once more.

If there is an r.f. meter at hand the aerial current

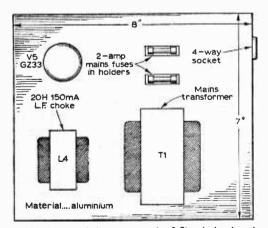


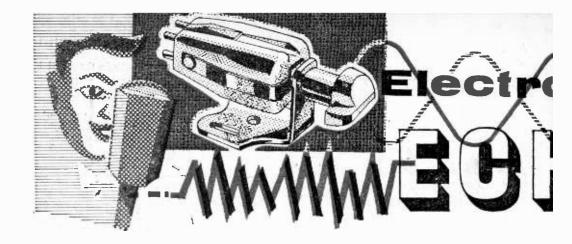
Fig. 5: Layout of the power pack of Fig. 4 showing the positions of components.

can be noted but if not, a bulb in the aerial lead will give some indication of aerial current.

AERIALS

Several different aerials were tried at the author's station but the half-size 5RV was found to be the best on 40m and a 160ft long wire on 80m.

COMPONENTS LIST
Resistors:
RI $47k\Omega \pm W$ R8 $25k\Omega \pm 2W$
$R2 25k\Omega 2W R9 10k\Omega 3W$
R3 50kΩ IW R10 100kΩ IW R4 100Ω IW R11 200Ω 2W
R4 100Ω IW R11 200Ω 2W R5 1kΩ 2W R12 10kΩ 3W
$R6 5k\Omega IW$ $R13 22k\Omega 2W$
R7 200Ω IW R14 25kΩ 2W
VRI 50kΩ wire-wound potentiometer
Capacitors:
C1 100pF mica C2 100pF mica
C3 100pF mica
C4 0.01µF paper 350V
C5 100pF mica
C6 0.01μF paper 350V
C7 0.01µF paper 350V C8 0.01µF paper 350V
C9 0.01µF paper 350V
C10 100pF mica
C11 100pF
C12 0-01 µF paper 350V
C13 0-01µF paper 500V C14 0-01µF paper 350V
CI5 100pF mica
C16 100pF mica
C17: 0-0 \(\mu \text{F} \) paper 500V C18 0-0 \(\mu \text{F} \) paper 500V
C18 0.01 \(\mu \) F paper 500V C19 0.01 \(\mu \) F paper 350V
C19 0.01 µF paper 350V C20 100 pF mica
Variable Capacitors:
VCI 20pF VC3 100pF
VC2 400pF VC4 500pF
VC5 1,000pF (2 x 500pF gang, parallel connected)
Coils:
LI, L2 see text
L3 16 turns spread over 2in. on 1½in.
former. Centre tapped.
VI EF91, 6AM6, or Z77 V3 6L6
V2 EF80 V4 807
Miscellaneous:
MI 100mA f.s.d. moving coil meter
RFCI-5 2.5mH r.f. chokes SI-4 Single-poie single-throw switch
SkI Coaxial socket
Jkl Jack socket
Power Supply Unit:
C21 16μF, 500V electrolytic C22 16μF, 500V electrolytic
L4 20H, 150mA choke
7! Mains transformer with tapped primary.
Secondaries: 400-0-400V 150mA; 6-3V
2·5A; 5V 2·5A V5 GZ33
FSI, 2 2A Fuses



HE unit to be described enables the popular reverberation or echo effect to be obtained with any audio signal source in conjunction with an amplifier. The method employed in obtaining this echo effect is rather unusual. insomuch that the device used for delaying the signal is electromechanical and does not use the recording technique with magnetic tape which is usual in this type of equipment.

The Delay Unit

This consists of two crystal pick-up units. type "Acos" GP71-3, as used in stereophonic gramophone pick-ups, with a series of metal springs between them. The springs are mounted so that they are coupled to the pick-up units at each end where the gramophone stylus used to be. (This is explained in more detail later in the text.)

If an audio signal is fed into one crystal unit the crystal itself vibrates and this vibration is coupled to the spring. The spring begins to vibrate in sympathy and, due to its mechanical inertia, the vibration takes a short time to reach the far end where the signal is reconverted into an electrical waveform by the other crystal unit. Thus the signal entering the first (or driver) crystal and the signal taken from the second (pick-up) crystal have a time delay between them, the length of the time delay depending entirely on the characteristics of the spring. If these two signals are fed simultaneously to an amplifier the effect heard will be

one of depth and space, adding a completely new dimension to the original sound source.

As it stands the effect obtained above has more the characteristics of reverberation than "echo", but to simulate the echo effect all that is required is to interrupt the delayed signal at a predetermined rate by a low-frequency oscillator. This gives a repetitive sound to the delayed signal and the overall effect is a repeated echo, the repetition of which can be altered by varying the interrupting oscillator frequency. Fig. 1 shows a block diagram of the complete system and will help the description above to be understood.

Electronic Section

There are three valves used in the electronic section of the unit and these are Mullard ECC83 twin triodes, making six separate functions in all. VI is a cascode R—C coupled amplifier used to bring the input signal up to a sufficient amplitude to drive the crystal unit on the delay chain. is no need for a gain control in this amplifier as the signal input is at a low level (i.e., from a microphone or electric guitar pick-up). One half of V2 is used as an amplifier for the pick-up crystal, the remaining section (V2b) is a cathode follower used to modulate the cathode circuit of this amplifier with the output of the low-frequency phase-shift oscillator. One half of V3 is employed as the oscillator and the remaining triode section is used as an amplifier for the direct signal path direct from the input terminals of the unit.

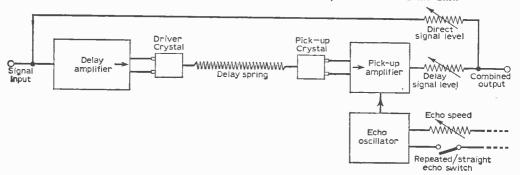
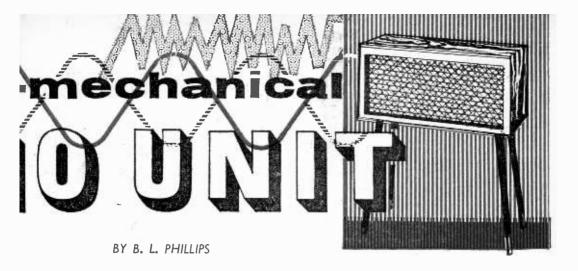


Fig. 1: Block diagram showing the basic requirements of the Echo Unit



Any form of power supply may be used, either a complete power pack built in with the rest of the unit or the supplies may be taken from the parent amplifier if they are available.

The requirements are an h.t. supply of 250 volts d.c., smoothed and filtered, and 6·3 volts a.c. for the filaments. The consumption is approximately 20mA h.t. and 0·9A l.t. A diagram is given for a built-in power pack and this method of supply is recommended as it avoids long leads carrying the supplies from an external source.

On no account is an a.c./d.c. type of power unit to be used with this unit. Apart from severe "hum" troubles this form of power supply is dangerous as it is virtually impossible to isolate all input and output leads and controls, etc., from the chassis. Again, if the supplies are taken from the parent amplifier this must be an a.c. only type with an isolating transformer incorporated.

Circuit Operation

The twin input jacks are matched for either high impedance microphones or musical instrument pick-ups or a combination of these. At the first grid of V1 the signal is "split" by a voltage divider network, a proportion is fed into V1a, the remainder to the grid of V3b (the direct signal amplifier). The two stages of V1 bring the signal up to a high level where it is fed to the drive crystal on the delay unit. The resulting mechanical vibration is reconverted in electrical impulses by the pick-up crystal and fed into the pick-up amplifier V2a.

The output of this stage is taken via a capacitor network $(3\times0.005\mu\text{F})$ to a gain control, VR3. This network is to remove any low-frequency component present when the echo repetition oscillator is in use; furthermore, the output of the network tends to rise with frequency and so removes any low-frequency noise due to external vibration of the delay unit. The $0.02\mu\text{F}$ capacitor across this network and chassis is a tone compensating device and may be any value between $0.005\mu\text{F}$ and $0.05\mu\text{F}$, depending on the output tone required. Without this component there may be a tendency for the unit to "squeal" similar to a microphone if it is placed too near the loudspeaker in the main amplifier.

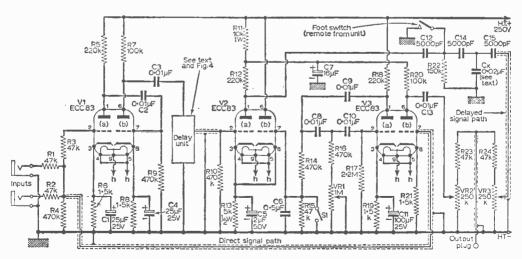


Fig. 2: The circuit diagram of the Echo Unit

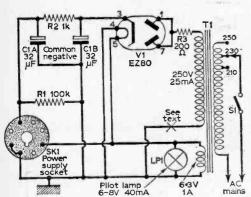
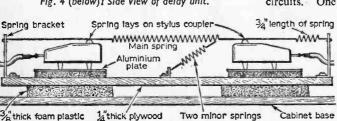


Fig. 3 (above): The power unit.
Fig. 4 (below): Side view of delay unit.

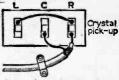


The repetition oscillator is coupled to the grid of V2b. Both cathodes of this valve are strapped together. Notice the value of the cathode decoupled capacitors (2µF); this has a low impedance at the signal frequency but allows sufficient low-frequency component to appear at the cathode from the oscillator. As this swings the cathode voltage the gain of the pick-up amplifier is varied in sympathy with the oscillator, giving a repetitive effect to the signal. The switch SI enables straight or repetitive echo to be obtained at will by interrupting the oscillator feed to V2b. The control VRI sets the speed of repetition between quite wide limits.

The two gain controls VR2 and VR3 set the level of the direct and delayed signals respectively, their outputs being combined and fed to a screened lead and plug for connection to the main amplifier.

Fig. 7 (right): Pick-up connections.

The entire echo unit can be silenced by placing a shorting switch across the socket marked "foot switch" and suitable switches are available



Cable clipped to wood base to prevent pulling on pick-up

at music shops dealing in electronic musical instruments.

Wiring Details

All connections should be short and direct and as far as possible components should be mounted as close to their respective valve-holders as possible. Screened lead should be used where indicated and the filaments should be wired in thin, tightly-twisted wire run away from the signal circuits. One side of the heaters is earthed to

chassis at the mains transformer or power input point. Do not earth one side of each valve heater and run a single filament lead as this will cause endless hum and noise problems.

The leads to the delay unit crystals must be screened and the springs themselves, together with the metal plate under the pick-up crystal must be grounded to chassis. It is better to run an earth

busbar along the chassis, earthed at the input jacks only, for earth connections. If any signal leads are longer than approximately $1\frac{1}{2}$ in. they are preferably screened, but if the recommended layout is followed, little trouble with hum will be had.

Case or Cabinet

This can be made out of any available workable material—i.e., wood, metal or even "Perspex" sheet. A plywood case is recommended for ease of construction, the front panel being metal and containing all controls and jack sockets, etc.

If covered in a "Rexine" or "Vynide" material the design suggested can look really professional, especially with the control panel done in a contrasting colour.

The internal delay unit is protected from mechanical vibration by its own flexible mounting (see delay unit construction) but additional protection for the whole unit can be given by placing four rubber feet in each corner of the cabinet.

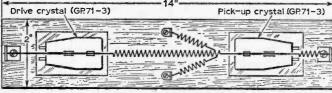
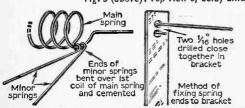


Fig. 5 (above): Top view of delay unit.

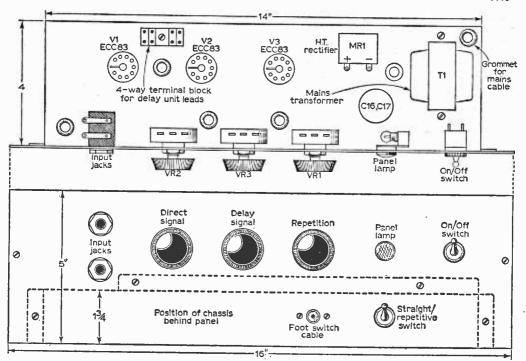


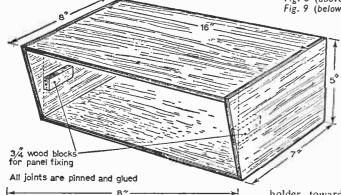
Delay Unit Construction

Fig. 6 (left):

Spring fixing.

of aluminium are cut just larger than the area the pick-ups cover. Each pick-up is attached to the metal base by cementing the three feet to the base with clear "Bostik" glue. When thoroughly dry two pieces of kin. thick foam plastic the same size as the aluminium plates are cemented lightly to the underside of each plate. Then the entire pick-up unit is cemented to the three-ply base so that they rest on the foam plastic





Note –
Panel Dimensions are for inside of cabinet

Chassis

Delay unit

Fig. 8 (above): Top view of chassis and control panel. Fig. 9 (below): Cabinet details.

supports. Allow approximately lin. clearance between the end of the plywood base and each pick-up unit.

The height between the wood and the top of the stylus couplers on each pick-up should be noted and two aluminium brackets made for the springs, each with two 18 in. holes drilled in them at the height where the spring leaves the stylus coupler and attaches to the bracket. Before mounting the brackets to the base remove the stylus on each pick-up by gently pulling the needle

up by gently pulling the needle holder towards the rear of the pick-ups with a pair of long-nosed pliers or tweezers.

The two small brackets are made in a similar method to the end ones except they are half the height of the former type, and they mount approximately in the centre of the wood base, one near each edge as shown on Fig. 5. Connect two lengths of thin single-core screened cable to the pick-up tags as in Fig. 7 and clip this cable to the wood base by means of a small metal U clip or staple, leaving some slack between this and the tags. The springs can now be fitted.

Spring "Doctoring"

The main spring is made up as follows: (1) Unwind about ½in. of one end of the spring and

-continued on page 1127

ig. 10: Position of delay unit and chassis inside the cabinet.

MAKING A

MUSICAL ALARM

Adapting a clock to automatically switch on a radio set at any predetermined time.

by W. R. Spence

NY reader who possesses a portable radio and would prefer to be awakened by the sound of soft music rather than the harsh clangour of the traditional alarm-clock may be interested in this device. Neither construction nor destruction is involved, only one straightforward piece of simple wiring being required. This is shown in Fig. 1.

On-off Switch

The on/off switch of the radio is by-passed by having the ends of a length of twin flex attached to the two terminal contacts. The switch must be left in the "Off" position. The circuit should then be checked by touching together the free ends of the flex, when the radio should start to function. Insulated wire, of course, must be used and the ends bared to make electrical continuity.

The idea is to use the hour hand of the clock itself as an automatic switch to operate the radio

at any predetermined time.

The end of one of the two wires in the flex is affixed to a convenient point of the casing, e.g., to the winding key. The end of the other wire must then be placed so as to make contact with the moving hour hand as the latter reaches the appropriate point on the dial. There are several

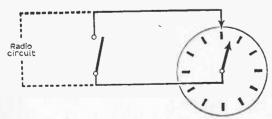


Fig. 1—Showing how the on-off switch of the radio is replaced by the hour hand of the clock. The bottom lead does not need to be connected to the spindle as metallic contact through any part of the frame suffices.

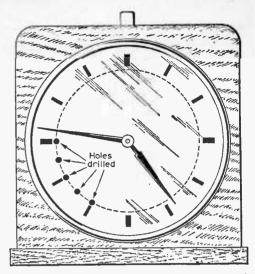


Fig. 2—The inner dotted circle indicates the line to be followed when drilling holes for inserting the end of the insulated lead.

ways of doing this, the easiest being to remove both the glass face and the minute hand. The following method, however, will be found to be both the neatest and the most effective.

As shown in Fig. 2 a tiny hole, the approximate diameter of the wire to be used, is drilled through the dial at hourly and half-hourly intervals. It is best from the point of view of neatness to do this for all 12 hours whether only a few are needed or not. The subsequent appearance of the clock is not affected unless it possesses an extremely short hour hand which does not quite reach the numerals.

Intermediate Positions

The unattached wire is then passed through the clock casing from the back and emerges from the hole nearest the time required. Intermediate positions between the hour and half hour are easily obtained by slightly bending the wire before inserting it and then rotating the wire in the hole until it assumes the position necessary.

Care has to be taken to ensure that the minute hand, which has to travel round the dial every hour, is not fouled by the contact for the hour hand and the correct position should be found by inspection. It is, naturally, important that good electrical contact be made between the hand and the wire as the pressure between them is very feeble. A painted or coated hand should be cleaned with sandpaper at the point where contact is to be made.

Alarm Switch

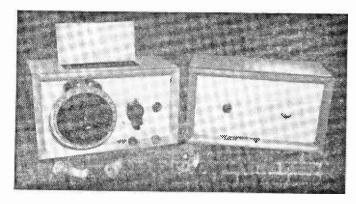
Although a switch is not essential, as the set wil switch itself off after a few minutes as the hanc travels forward, it is advisable to fit one. The same time does occur twice in the one day and it could be disconcerting to find the radio un expectedly coming to life in the evenings.

The Twin-Unit Two

PART ONE

A PAIR OF EASILY MADE MATCHING UNITS WHICH COMPRISE A SIMPLE RECEIVER AND A POWER UNIT

A, Sydenham



DESPITE the simple circuitry employed, this pair of matching units can, when used together, provide a remarkably wide range of listening enjoyment. As may be seen from the photographs, the units are small physically and both are easy to construct. Either unit may be both are easy to construct. Either unit may be built independently of the other, for some readers might find Unit "A" of interest, while others do

not and vice versa.
Unit "A" is Unit "A" is a simple two-stage receiver constructed originally to provide headphone reception of signals transmitted in

the bands from 0.5Mc/s to 15Mc/s (20-560m approximately), where much of interest is obtainable, since many amateur bands are contained therein. Tuning is continuous, due to the use of ready-

made plug-in coils.
Unit "B" is a simple power unit and although it is intended orimarily for use with Unit "A t can also be used for other purposes if this does not involve heavy

current demands.

Although Unit "B" is not generally required if a power pack s already available, beginners night not be so well equipped and he inclusion here makes for completeness. As presented both units ire safe to handle at all times, due o the inclusion of a mains isolatng transformer, but should the eceiver be used with a different ype of power supply unit, care hould be taken to ensure that it is uitably insulated from the mains upply.

The Receiver

Circuit details are given in ig. I where VIA operates as

a grid leak detector-cum-audio amplifier, with V1B providing increased a.f. amplification. Signals are conveyed to the tuned circuit inductively from the aerial, a variable trimmer, TC1, being fitted so that best results can be obtained. Band changing is, as was mentioned earlier, by the "plug-in" method, and coils from the well-known Denco range have been chosen since these conveniently fit a standard Noval valveholder. The coils are designed to operate in conjunction with a tuning capacitor of 300pF

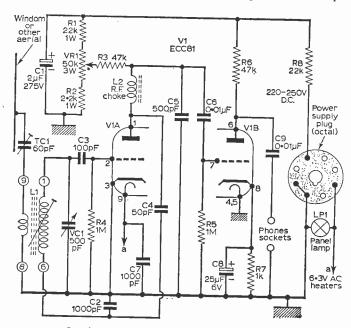


Fig. 1: The circuit diagram of the receiver unit.

(nominal) value and this fits in nicely with the arrangements used as will be seen later.

The circled figures associated with L1 in Fig. 1 refer to the coil spills and also coincide with the appropriate pins on the Noval valve base into which they are inserted as required.

Considering the circuitry associated with VIA it will be noted that the cathode of this section is connected to a capacitive potentiometer connected across the coil. the "outers" of which are taken to the grid and anode of the valve. Due to C5 the anode is "earthy" and when operating conditions are suitably adjusted positive feedback results, the r.f. choke L2 assisting the function. Control may be effected by varying the applied potentials and this is done by manipulating the potentiometer VC1, which is inserted on the "hot" side of the anode feed resistor R3. By using the VC1 judiciously V1A may be pushed smoothly to its most sensitive operating point—viz., to the edge of oscillation. Detector sensitivity is thus stimulated and tuning sharpened-but clumsy handling of the control will either (a) ensure low sensitivity or (b) cause unwanted and undesirable oscillation. It may be noted here that in an earlier temporary "hook up" the r.f. choke was exchanged for a 33kΩ resistor in an attempt at economy, but inferior results were obtained.

Tuning Capacitance

The effect of capacitively tapping the coil causes its tuning range to be restricted since the maximum external capacitance across it must always be less than the smallest value used due to the series connection. The problem is resolved here, however, by choosing values of 500pF and 1,000pF for VC1 and C2 respectively, thus reducing the overall maximum tuning capacitance to that recommended by the coil maker. Other types of regeneration circuit are possible, of course, but here the primary winding of the coil is left free for aerial connection purposes.

An alternative method of regeneration

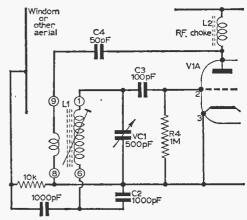


Fig. 2: This shows an alternative arrangement for obtaining regeneration.

depicted in Fig. 2 and here feedback is taken to the coil primary winding, thus necessitating an alternative method of connecting the aerial, which may be taken to the "bottom" of the tuned winding as shown. Another method of controlling regeneration is to adopt the circuitry of Fig. 2 but to make C4 a 500pF (maximum) variable capacitor and in this case VC1, R1 and R2 (Fig. 1) can be omitted, R3 being connected direct to the h.t. line. A variation, and one that confers greater gain at the expense of selectivity, is to ground tag 6 and to feed the aerial via a trimmer to tag 1, but in this case VC1 should be reduced in value to 300pF (nominal). In general, component values relating to Fig. 2 circuitry should agree with those specified for Fig. 1 except where otherwise marked.

The operation of V1B is simple enough to warrant no explanation but it will be noted that the parallel-fed phone outlet provides safety to the

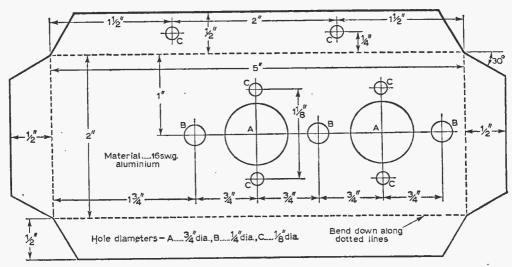


Fig. 3: Chassis drilling details for the receiver unit.

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user since d.c. is blocked off. The receiver is not fitted with an on/off switch since this is contained in Unit "B".

# Mechanical and Constructional Notes

The smallness of the unit makes it possible to use a simple aluminium "tray" chassis which is secured to a hardboard panel that carries the simple controls together with a coloured warning lens, reduction drive mechanism and phone sockets. Details of both the panel and the chassis are given in Figs. 3 and 4 respectively and are self-explanatory, although the actual panel should be cut \$\frac{1}{2}\$ in smaller

panel should be cut tin. smaller than the horizontal dimension given and tin. shorter than the vertical dimension because the tin. quadrant which is glued as a frame to the panel edges is allowed to overlap to form a rabbet for the simple cabinet side and top members; the quadrant should be mitred at the corners, of course, and the bottom section routed out to receive the phone sockets. Metal cooking foil glued to the inside of the panel and in contact with the chassis prevents unwanted hand effects from interfering with operation. Although the trimmer TC1 and the aerial socket may be mounted on the chassis rear flange these are affixed to the cabinet back in the prototype and fitted with a flexible lead.

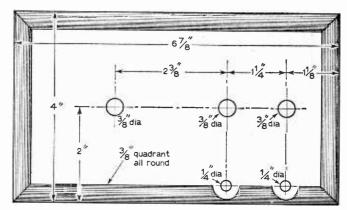
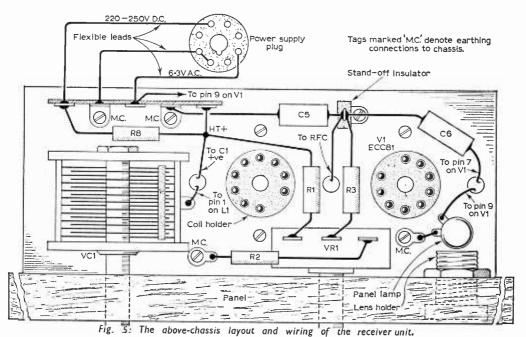


Fig. 4: Details of the panel of the receiver unit.

Diagrams showing the above and below chassis layout and wiring are given in Figs. 5 and 6 respectively and show that modern miniature components are fitted to prevent congestion. L2 is also physically slim and mounted not as shown in Fig. 5 (so drawn to assist clarity) but turned through 180deg, with the connections close to the chassis.

## Power Cable

It is convenient to obtain the voltage supplies via a three-core cable terminated with a standard octal plug to fit a socket provided for it on Unit "B" (to be described later) and the idea is shown diagrammatically in Fig. 5, where it can be



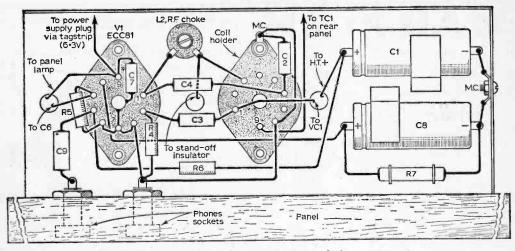


Fig. 6: The under-chassis layout and wiring of the receiver unit.

seen that the receiver end of the cable is connected to a simple tag strip to which the various feeds are connected. A suitable plug can be obtained by placing an unwanted octal-based valve in a strong paper bag to obviate flying glass splinters and tapping it smartly with a hammer!

The orientation of the valve bases permits short wiring and a spare tag on the coil-holder is

utilised as an anchor for the choke L2, this item consisting—since it needs to be physically small—of a miniature dust-cored long waveband coil sawn off to the length of the core and with the primary winding removed.

Part Two next month will describe the power unit and testing.

# ELECTRO-MECHANICAL ECHO UNIT

-continued-

pull it straight, make a small hook on this straight piece and carefully insert through the holes in the bracket at the pick-up crystal end. Pull the spring gently straight over the pick-up (without stretching it too much) and note where the spring meets the rear of the pick-up. Leaving about \(\frac{1}{2}\) in. of coiled spring between the bracket and the rear of the pick-up, unwind sufficient wire so that a straight length appears over the length of the pick-up—over the stylus coupler. Allow enough to clear the pick-up at each end by about \(\frac{1}{2}\) in.

(2) Now hold the spring (still attached to the bracket) over the drive crystal and again note the position on it about \(\frac{1}{2}\)in. from the edge of the drive crystal. From this position to past the other bracket straighten out the coil so that another straight length of wire appears over this pick-up and stylus coupler. Insert this straight end into the bracket holes and after pulling just enough to keep the spring from sagging too much in its centre make fast on the bracket.

(3) The two small springs are made in a similar way, leaving enough straight wire where they join the main spring so that the small springs do not touch the main one along their length. The tension on these springs should be very low, in fact just enough to hook them over the main one so that they don't pull on the small \{\frac{1}{4}\times \text{. coil}\ at the pick-up crystal end and cause it to foul the end of this pick-up.

(4) Making sure the main spring lays in each stylus coupler, a small dab of clear cement will hold them in place. Another dab of cement keeps the small springs in place on the main one.

To reduce hum it is advised that one spring bracket and the plate under the pick-up crystal be returned to chassis via the screening on the pick-up lead. Small solder tags bolted to these and connections made with thin flex will suffice.

The type of spring material used in the prototype consisted of an electric fire element obtained on a card in any electrical shop. The lightest one available should be used, the gauge being about 36 s.w.g. The more highly tempered the spring the better will be its characteristics—but it must be light and have a very close coil arrangement.

### Operation of Unit

Connect any convenient signal source to one of the input jacks and couple the output lead to the input of the main amplifier. Set the volume of this amplifier roughly to mid position. Set VR2 (direct signal gain) until the volume is adequate and with the straight/repetitive switch in the "straight" position increase the setting of VR3 until the reproduced signal sounds "echoy" of hollow. This is the reverberation effect. If the echo sound is rather shrill or "toppy" increase the valve of CX (Fig. 2) until it sounds satisfactory. Switching to "repetitive" will introduce the staccato effect to the delayed signal, giving a pleasing "true" echo sound. By reducing the direct signal level it is possible to use the echo signal alone for added effects.

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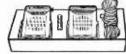
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But even a meter movement taking such a low current as  $10\mu$ A for full-scale deflection, as used in an instrument with a sensitivity of  $100,000\Omega$  per volt, can have an appreciable effect on a circuit with a high impedance.

# Damping Effect

For example, if we apply the test probes of our meter to a battery we should expect to obtain an accurate reading because the internal resistance of the battery is very low compared with the resistance of the meter.

Similarly, measuring the grid bias of an amplifying valve by applying the meter across the cathode bias resistor should also produce accurate results. But if we now apply the meter to the true grid circuit it is unlikely that the test would be successful; the grid leak resistor may be as high as  $1\text{M}\Omega$  and we are shunting it with a meter resistance comparable in value if we use the 10V range of our meter to give us a readable deflection.

Switching the multimeter to a higher voltage range reduces the shunting effect but limits the swing of the pointer to a small sector of the scale.

#### A.C. Errors

Similarly, small voltage measurements in an a.c. circuit of high impedance, such as the detector circuit of a radio receiver, can be even more misleading. Indeed, the connecting of a meter across many such circuits is sufficient to upset their operation and thus render our readings useless.

As we have noted, the sensitivity of the multimeter built around a basic moving-coil movement is considerably less for its a.c. ranges. Also the waveform of the voltage under test and its frequency will affect the accuracy of the reading.

Where a.c. measurement is obtained by rectification and subsequent d.c. movement—the normal method—the non-linear characteristics of the rectifier unit must be taken into account.

The higher the frequency being measured the more is the by-passing effect of the meter rectifier and the less accurate the reading. Also, as most meters are calibrated in terms of the root-mean-square value of the applied voltage or current, any deviation from a sinusoidal waveform will alter the ratio and a square wave will give what is almost a d.c. reading, whereas a "spiky" waveform will cause the meter to read low.

The answer to the problem is a meter having

negligible loading effect on the circuit under test and with only a very small capacitative loading that would tend to shunt the higher frequencies. Such an instrument is the valve voltmeter.

## Principle of the VTVM

The basic principle is the application of the test voltage to the grid of a valve which is part of a bridge circuit with a meter reading the "out-of-balance" current of the bridge. Thus the applied voltage is "looking into" the very high impedance and small capacitative shunting effect of the input grid.

The bridge is first balanced, the meter "zeroed" and the resulting change of conditions from the application of the test voltage causes an unbalance and a proportionate meter reading.

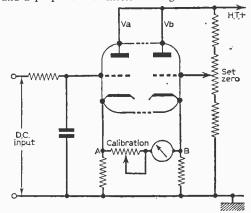


Fig. 10: Basic circuit of a valve voltmeter.

As shown in Fig. 10 this is a d.c. function. The valve is connected as a cathode follower amplifier with each half passing the same current when no test voltage is applied, the set zero control being used to regulate the bias of Vb under these conditions. Then the voltages across the cathode resistors of Va and Vb will be the same and the meter will not deflect.

Applying a test voltage to the terminals, with negative polarity to chassis, will cause Va to conduct greater current, producing a greater voltage across the cathode resistor. Thus point A is now of higher potential than point B and the meter pointer will deflect in proportion to this voltage difference.

A calibrating resistor acts as a multiplier to keep the meter reading within limits of the change in bias voltage. Correct choice of components to match the valve characteristics will result in linear calibration.

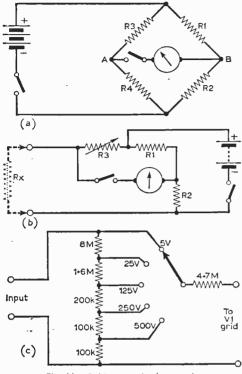


Fig. 11: Bridge circuits (see text).

Experienced readers will now prepare to jump on me for over-simplification. The foregoing is a basic explanation of the operation of the circuit. A more explicit answer to the question "What happens when a voltage is applied?" requires the addition of a few notes on bridge characteristics. Talking of balanced and unbalanced bridges is

a waste of time unless we define our terms and the understanding of bridge circuitry will prove handy later when we come to consider some applications of signal generators and oscilloscopes and a.c. bridges proper.

April, 1963

## The Wheatstone Bridge

If four resistors of equal value are connected across a supply voltage as shown in Fig. 11(a) and a meter linked to the midpoint of each arm there would be no deflection of the pointer.

This is because the current flowing in each arm of the circuit—that is, through R1+R2 and R3+R4—is the same; therefore the voltage dropped across R1 and R3 is the same and points A and B are at the same potential. So the meter does not record and the bridge network is said to be balanced.

If we now substitute R4 with a resistor of unknown value-and if that value differs from the original—the condition of balance will be upset and there will be an indication on the meter. If R3 is now made variable and its resistance is measured, then by adjusting R3 until the balance is restored, and the meter again shows no deflection, we have a method of determining the value of the unknown resistor Rx.

Fig. 11(b) shows the circuit in a different form -principally to demonstrate that bridge circuits are not always immediately recognisable by that characteristic diamond shape of the resistor

Bridge-type circuits are widely used in radio work and it is not always obvious at a glance that the form of the circuit is indeed the familiar bridge. One must mentally translate the draughtsman's work to recognise circuits.

## The Unknown Resistor

The formula for determining the value of the unknown resistor when the bridge is balanced is: R2-R3 R1

In practice  $\frac{R2}{R1}$  would be a constant and the value

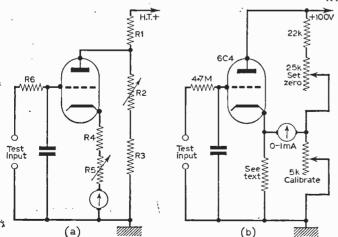


Fig. 12: The use of a valve to amplify an applied voltage and give a meter indication.

of Rx would be that constant multiplied by the resistance of R3 required for balance. This application will be more useful to us we consider bridge-type instruments. In the meantime it is only necessary to remember that our meter is reading an "unbalance" current.

Now let us substitute R3 with a valve and feed our test voltage between its grid and cathode. First, disconnecting the terminals and adjusting the set zero control, we arrange that the bridge is balanced and the valve acts as one resistive arm of the bridge.

Now we apply a d.c. test voltage, the valve's anode current changes and thus its Ra value. The resistance of our substitute R3 has thus changed and the meter will give an unbalanced indication proportional

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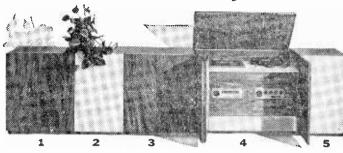


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to the change in R3 or the input volts.

#### Anode Current Meter

This type of circuit is very little different from the "old-fashioned" idea of using a valve to amplify the applied voltage, with a meter indicating the change in anode current. A circuit of this type is shown in Fig. 12(a). The anode of the triode valve is fed from a tapping on a potentiometer across the h.t. consisting of R1, R2 and R3.

The centre resistor is made variable and acts as a set zero control. R4 and R5 in series with the meter provide standing bias, with R5 variable to give a measure of calibration and R4 a fixed value, limiting the current to the straight portion of the

valve characteristic.

The limitations of this device are obvious and Fig. 12(b) shows a development that more nearly approaches the bridge circuit. This is a useful

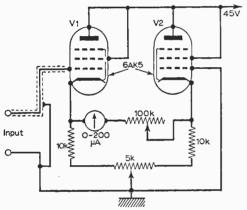


Fig. 13: Practical valve voltmeter circuit.

circuit that can be built easily around a valve such as the 6C4, 6C5, EF91 or EF80. The cathode resistor would have to be chosen to give a linear indication for the particular valve in use.

The range of voltages that can be measured by this method may be selected by a switched potentiometer input such as in Fig. 11(c). The input resistance is equal to the total of the potentiometer,

usually  $11M\Omega$ , on d.c. ranges.

An important point is that this load on the circuit being tested remains practically constant for all ranges, a further limiting resistor of high value, between 1 and  $5.5M\Omega$ , being connected in series with the input to the valve grid. See R6 in Fig. 12(a).

In the commercial instrument these resistors forming the potentiometer are high-stability components specially formed to give accurate proportion of network resistance and not generally of preferred values. The experimenter wishing to make up a circuit such as Fig. 12(b) may find it better to compromise with a  $10M\Omega$  input using valves as indicated.

# High Input Impedance

Some valve voltmeters have input impedances up to  $25M\Omega$  on the d.cs. ranges. Going even higher, the interesting circuit of Fig. 13 gives an

input impedance higher than  $100M\Omega$ , high enough for accurate measurement of small voltages across the high resistors found in modern equip-

This was first described in the January, 1957, number of Radio and Television News and is an American design by D. G. Shankland. The important factor is the use of valves with a very low grid current. The 6AK5 valve of Fig. 13 has a grid current of  $10^{-4}\mu A$ . The voltage difference between the cathodes of the two similar valves is read by the 200µA meter.

The test voltage is applied to the grid of V1 via a probe with a series resistor in the "live" lead of not less than  $10M\Omega$  and the grid of V2 is returned to chassis. Under these conditions, with no signal input, the  $5k\Omega$  preset resistor is used to set zero to compensate for slight differences in valve characteristics, supply voltages, etc.

Full-scale deflection of the meter indicates an input of 20V. The relevant cathode voltage is expressed by  $1/(1+\frac{1}{\mu})V$  where  $\mu$  is the amplification factor of the valve, a high figure in this case, and V the input test voltage.

The provision of a calibrating resistor of  $10,000\Omega$ in series with the meter helps to compensate for the  $1/\mu$  term and, provided care is taken in construction to avoid leakage across the input, very accurate voltages can be read.

Normal practice is to take the input lead through the casing of the instrument to the grid of V1 via a porcelain feed-through insulator.

## A.C. Applications

Mention of a probe in the last description brings us to the important question of the measurement of alternating voltages. Here there are several restrictions. The instrument must again impose as small a load upon the circuit as can be obtained—and the standard multimeter has severe limitations on a.c. as noted in the previous articles.

But in addition to a high input impedance the valve voltmeter, or electronic testmeter, must have a small shunt capacitance and be capable of handling a wide frequency range. Although one or more valves may be used as buffers between the input signal and the point of measurement, connecting circuits themselves tend to restrict the frequency response by capacitative and inductive leakage. It is necessary, therefore, to rectify the a.c. signal as near the test source as possible and, feed the resultant d.c. to the meter proper. Consequently much research has gone into probe cir-cuitry and construction and a number of ingenious devices are on the market. It is possible to rectify a few millivolts at frequencies up to 200Mc/s, amplify the resulting signal sufficiently to load the input to the main meter and obtain readings of remarkable accuracy. Fig. 14 shows typical examples of these probes with both valve and crystal rectification.

#### Crystal Rectifler

The simplest type, which can be built into a handy casing such as a discarded fountain-pen holder, consists of a crystal rectifier, its charge capacitor C1 and filter components R1, C2 as in (a). Slightly more elaborate is the circuit of (b), which has a crystal connected in opposite sense, giving a negative-going output suitable for feeding

a transistor amplifier.

Note that the charge resistor R1 has a high value, the time constant of the C1, R1 combination being carefully chosen to give the most accurate results over a wide frequency range. This is usually decided by the function of the instrument and an alternative probe with a smaller value of C1 may be provided for r.f. measurement. For example, in the AVO electronic testmeter C1 is 0.05 µF for the audio ranges and 470 pF for radio frequency measurement. The Taylor 171A uses  $0.01\mu F$  and 1.000pF, with a leak resistor of  $20M\Omega$ .

Both of these commercial instruments have valve rectifier probes in their original versions and

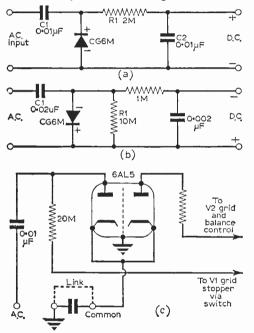


Fig. 14: Typical examples of crystal and valve probes.

the probe circuit of the latter is chosen to illustrate the typical valve method at Fig. 14(c). One interesting point is the use of a double diode valve. with one diode connected back to the control grid of the second triode in the bridge. The rectifier is a 6AL5 (EB91) and the double triode a 12AU7 (ECC82). The purpose of this circuit is the correction of a.c. set zero, which is adversely affected by "contact potential".

#### **Electro-Chemical Action**

As the name implies, contact potential is the effect of electro-chemical action due to the physical construction of the valve and its base and connections at the higher frequencies. A small voltage is developed across the load even when no external test voltage is applied. This needs to be backed off, or neutralised, to avoid the annoyance of a

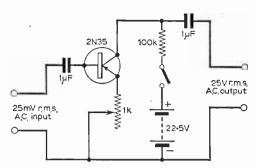


Fig. 15: Transistorised a.c. probe.

small standing deflection of the instrument pointer when the a.c. ranges are used. Thus by using a second diode and circuitry in such a manner that the contact potentials of the two sections of the valve cancel out, and biasing the valve by returning the leak resistor to a slightly positive point, an accurate set zero can be made on the a.c. ranges.

To further compensate for the non-linearity of the diode a preset control in this feedback circuit, called the diode balance, gives a small shift on the lowest range. The AVO model has a rather different arrangement, but with the same purpose, and allows a 0.07V standing reading on the lowest a.c. range, which is quite normal. From this it can be readily understood that the instrument is sensitive to very small a.c. voltages and therefore certain precautions are necessary in its use.

#### Short Connections

On the Taylor 171A, for example, using a 2.5V a.c. range, an absorption of only  $25\mu W$  from an external field will give full-scale deflection. Connections to the source must be kept as short as possible. The low-level connection should be bonded to the chassis or low-level point of the apparatus under test (making sure when checking a.c./d.c. equipment that the chassis is at neutral

potential, not live). An external shorting link is often provided for protection where the low-level connection of the instrument is not bonded to its own casing and should be used where applicable. There should not exist a high potential difference between the negative terminal and the chassis. It is often advisable, for instrument protection, to make the negative connection first before applying the probe to the circuit under test and to keep the input terminals short-circuited on the low-voltage ranges until the tests are to be made. This danger of stray pick-up and sudden meter deflections is not so marked on the modern instruments but should be avoided as a matter of course.

Similarly, the strictures given before about commencing test measurements on the highest voltage range and resetting to the appropriate range also

apply to the valve voltmeter.

When measuring voltages with waveforms that may not be sinusoidal special care is required. Meter deflection is generally proportional to peak values of the a.c. input, although the scale of the meter may be calibrated in r.m.s. values. Reference to Fig. 14(b) makes this clearer.

—Continued on page 1133

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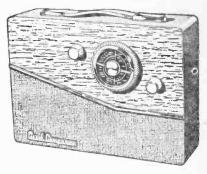
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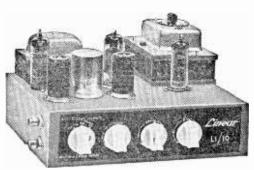
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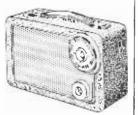
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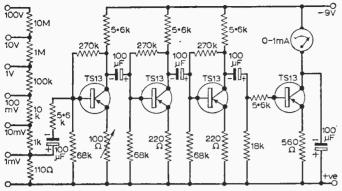


Fig. 16: The Brimar transistor voltmeter.

When a.c. is applied to the probe the rectifying action charges up C1 to the value of the peak voltage. During negative half-cycles the charge tends to leak away, but the time constant of C1 and R1 is such that, even at the lowest frequency to be handled, the next peak charges C1 before the previous charge has time to leak away.

The result is that after filtering by the  $1M\Omega$  resistor and  $0.002\mu F$  by-pass capacitor a d.c. voltage tending to follow the peaks is applied to the meter. But the "averaging" process of peak reading is such that accurate calibration in r.m.s. values only applies when a truly sinusoidal waveform is being measured. Peak voltage is then 1.414 times the indicated r.m.s. When a nonsinusoidal input is being probed the rectified d.c. will be an average of the peaks and not always a trustworthy indication of potential.

For this reason, when testing an a.c. voltage that may not be a sine wave, check for "turnover error". This is the effect of, say, a large positive peak and a small negative peak such as an asymmetric waveform would produce. Reverse the probe connections and the meter polarity and note that readings though opposite should be similar in value. As a further precaution make a series of spot readings before and after reversing the connections and compute an average result. Check the set zero control both before and after the test and whenever the range switch is changed.

For measuring small a.c. voltages switch to the lowest range and short-circuit the probes before zeroing to eliminate the risk of false readings due to stray pick-up. Many commercial instruments have facilities for meter polarity reversal; constructors will find that the little extra trouble and cost of fitting a double-pole switch is well repaid.

#### Millivoltmeters

A good-quality instrument will measure quite small voltages but for really accurate low potential readings a valve millivoltmeter may be necessary. This is a slightly different instrument in that it has a wide-band amplifier incorporated. The a.c. input is fed through several stages, often cascode coupled and with heavy negative feedback to improve stability and retain response.

Typical of such instruments is the Advance 77, which has a full-scale deflection of 1mV and gives a useful indication down to 100 µV.

In instruments of this type the amplifier may also be used independently, making a very versatile piece of equipment, especially for audio work, where the millivoltmeter finds a special usefulness as a decibel meter. An example would be the use of the millivoltmeter amplifier as a Y-amplifier for scoping particularly small voltages to obtain a usable trace.

Another very popular example is the Heathkit model AV-3U, which has a full-scale deflection of 10mV on the lower range and a scale that gives a trustworthy indication down to a millivolt. The

input impedance is  $1M\Omega$  at 1,000c/s and the circuit consists of a cathode-follower input stage feeding a cascode amplifier which drives another cathode-follower and an amplifier into a bridge rectifier across which the meter is balanced.

## Transistor Instruments

Because of the amplifier facility this type of instrument is suitable only for alternating voltages. Some interesting developments have been made by the use of transistors for amplifier probes to extend ranges of low-volts/high-impedance meters. One such example is seen at Fig. 15 where a single transistor gives a gain of 1,000 in a simple circuit that can be built in a probe.

More ambitious, yet quite straightforward in circuitry, is the Brimar Transistor Voltmeter illustrated in Fig. 16. Six ranges between 1mV and 100V feed a three-stage amplifier of conventional common emitter mode, driving an output transistor whose variation in collector current is measured to provide an indication. Input impedance is better than  $11M\Omega$  on the top volts range.

Another interesting circuit is that of the sensitive d.c. transistorised voltmeter originally published in the Mullard book *Transistors for the Experi-*

This instrument has four OC71 transistors, two connected in common collector and two in common emitter fashion, with the input voltage applied between the bases of the former pair. A 20mV input gives full-scale deflection of the  $100\mu A$  meter movement and the input impedance is  $1M\Omega$  per volt. To extend the range of this device series resistors would be required.

It should be remembered that the virtue of transistor circuitry is that from a low-impedance input, with grounded collector giving a linear characteristic, the emitter current is proportional to the input voltage (and to  $\alpha'$  times the input current—which in this case is between half and  $1.5\mu A$ ). This output can be applied to the common emitter pair having the normal low-impedance input characteristic, giving an unbalance reading on a microammeter connected between collectors proportional to the applied d.c.

PART 4 OF THIS SERIES APPEARS NEXT MONTH

By THERMION



HAVE already received a number of letters regarding my comments in last month's issue on old sets. One point which has been raised concerns the loudspeakers which were used in my conversion, but this has brought to light one of my pet moans concerning the radio industry—one which I have before mentioned, and which has been with me for as long as I can remember.

### Unmarked Components

Those of you who have a fair sized spares box I ask to go through it and see how many items carry any indication of the value or the maker. 1% or even less, I guarantee. Look at all the variable capacitors you have, either the old largesize type or the more modern midget components, and you will not find any indication as to the maximum capacity.

How many loudspeakers have you? Do you know the impedance, or even the maker? Yet, in view of the importance of these two items, not to mention the many others that there are, one would expect such information to be clearly marked somewhere. The end plate could be stamped on the capacitors and the impedance could easily be stamped on the frame or the magnet of the loudspeaker.

One would have thought that makers would have been only too willing to print their name or trademark on their products (if they are proud of them).

The greatly increased use of the transparent sticky tape should have led to a protected form or marking and this I now do in many cases with bits and pieces which I put in my spares box, and where the size permits I endeavour to include some data concerning previous use. This naturally is in the form of a code but it helps when going to use the item again.

# Valve Substitutes

Looking through a batch of readers' queries for the past year, it is surprising how many readers were interested in finding valve substitutes—either for a set of early vintage which they were modernising, or because they had stocks which they wished to use in place of a specified item.

The modernising of an old set, by the substi-

tution of modern midget valves to replace the older valves, is one which often leads to disappointment, mainly because it is found that the modern valve is a much more efficient component than the old one, and this leads to the necessity for some circuit re-arrangement, and this sometimes amounts almost to a re-build of the set, to keep it stable.

One type of replacement which I have found almost faultless is the use of ECC82's (12AU7's) in place of 6SN7's, and ECC83's (12AX7's) in place of 6SL7's. In no circuit where the latter types have been specified have I found it impossible to use the former, but there is no other valve replacement of this type which I have found so definite and effective.

If you are thinking of making a valve substitution of this type try and make it a general rule that the modern midget is a much more efficient item than its old time large counterpart—although the characteristics appear more or less the same.

## Modernising an Old Set

Another point which seems to crop up rather frequently is the modernising of the old type of set which had a line cord and was of the midget type at one time very popular in America.

The output valve in these sets consisted of a double valve—output pentode plus half-wave rectifier. This type of valve no longer seems available and with the difficulty of the line cord a conversion worth considering is to fit a half-wave metal rectifier and use the a.c.-d.c. technique. It is essential, however, to make sure that the control knobs are properly insulated (the case is usually moulded bakelite), the mains lead properly anchored and if necessary any grub screws in the knobs filled with wax.

A small piece of wood will hold the rectifier, either bolted to the chassis or wedged between the chassis and the cabinet, and then an ordinary output pentode may be used with the wiring adjusted as necessary.

If you consider this type of conversion, however, bear in mind that this type of set is essentially portable and may be carried from room to room, and if the cardboard back of the cabinet has become lost or badly damaged make a new one from hardboard or thin plastic and take every precaution to guard against fingers etc. coming into contact with any metal on the set. This includes the end of the throw-out aerial with which these sets are usually provided.

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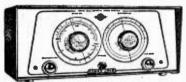
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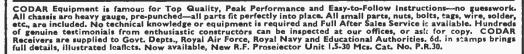
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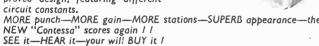
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# Letters to the Editor

The Editor does not necessarily agree with the opinions expressed by his correspondents

Whilst we are always pleased to assist readers with their technical difficulties, we regret that we are unable to supply diagrams or provide instructions for modifying commercial or surplus equipment. We cannot supply alternative details for receivers described in these pages. WE CANNOT UNDERTAKE TO ANSWER QUERIES OVER THE TELEPHONE. If a postal reply is required a stamped and addressed envelope must be enclosed with the coupon from page iii of the cover.

#### WHAT ABOUT THE LONE-WOLVES?

SIR,—As a reader of P.W. for some years now I would like to air some views arising from reading the article "Coronation Street or CQ.ZL" on the Club News page of the February issue.

The good advice therein obviously must apply expressly to prospective "ham" transmitters and the sentiment in reference to lone-wolves truly describes their possible position while not being members of a club. But what of the vast number of lone-wolves who have no desire to become licensed operators, but have a lively interest in the greater, more varied and ever advancing general application of associated electronics.

They too, of course, should join a club and quickly ascertain whether their own particular needs can be fully realised. For them I venture to suggest the name "Radio Club" can be somewhat misleading in many instances of the smaller local organisations, where it may be found that the dominant moving spirit is always around these members who are active operators, while all other functions are apt to take on a much lighter and

subsidiary character.

Typical music-hall jokes on golfers, anglers, motorists, etc., in the pursuit of their respective hobbies are no more humorous than the spectacle of tangled multi-arrays, rhombics, ground planes and doubtful looking towers; much of which represents a laborious effort to keep up with the Jones's of radio when the "rig" can be described as so many hundred feet of wire fed with a lamentable low power stipulated in the terms of the licence. Included will be a receiver the

figures in the pounds column.

Upon hearing such a "run down" the possessors of less ambitious equipment must sometimes feel like changing over to Bingo for relaxation. To them should go a clarion call "take heart" and to you chaps with the banks of "813's" in parallel, raise your hats to some lone-wolf who is working a diminutive transistor "rig", emitting a few milliwatts on centimetric frequencies.—P.

purchase price of which runs into three good

#### SOMETHING UNIQUE

ASHDOWN (Newton-le-Willows, Lancashire).

SIR.—May I take this opportunify to thank you for publishing the article "Electronic Metronome", which appeared in the February

issue. This instrument used only a very simple circuit and for a not very musically-minded person like myself had little practical use, but personally, I found this tiny unit had great value in the fact that here, for once, was something different, something almost unique, which provided a most welcome change from the usual receivers, oscilloscopes, amplifiers, etc., etc.

In the same issue was another such article. I don't suppose I shall ever want or make an echo chamber, but I must confess that I read B. M. Jeffery's article on this subject, twice and found it full of interest both times.—A. M. HEADLEY (Bradford, Yorkshire).

#### HI-FI FANATICS

SIR,—I have followed the correspondence on Hi-fi Fanatics with interest and I can only wonder why Mr. Maitland and the other enthusiasts do not treat themselves to a stereo tape deck and pre-amplifier.

It has always struck me that the present popular disc method of reproduction is a most unfortunate evolution of the horn and sound box era. The quality of a good commercial stereo tape recording has to be heard to be believed; its life is almost infinite; there is no falling off of quality towards the end of the recording (as with disc records) and dust and cleaning worries can almost be forgotten, except for occasional wiping of the tape head.

The main disadvantage is, of course, that the commercial stereo tape recordings are expensive by comparison with disc, but this is largely because of limited demand.

As a matter of interest, I built my own stereotape equipment for about £40 and I consider it gives superior reproduction to a friend's disc equipment costing over £150.—R. C. HAWKINS (Ramsgate, Kent).

#### GOING MOBILE

SIR,—It is some years now since I first started operating my own rig and for most of this time my wife has held a grudge over my transmitter, receiver and ancillary equipment which—because we live in a flat of restricted size—I have to keep and use in the bedroom. Her main objection is that the units cannot be moved as a whole and by virtue of the fact that most of them are connected by cables, they cannot be moved individually. This situation used to present a problem when cleaning and dusting operations were in progress, until recently I found the solution by utilising a metal tea-trolley as a mobile workbench-cum-operating desk. My only worry now is, should I apply to the GPO for a mebile licence?—J. Willis (Liverpool).





A spares sale was held on February 15th and it is intended to operate the Club transmitter (call-sign G30AM) on most club nights.

BURTON-UPON-TRENT AND DISTRICT RADIO SOCIETY

Hon. Sec.: H. Harrison, 38 Baker Street, Burton-upon-Trent, Staffordshire.

A recent lecture on the "Radio Control of Models" was given by Mr. Arthur Fallon.

At the main meeting for February, held on the 13th, W. Hazelden, the Society's chairman, gave another talk on "Single Sidehand"

Potential members and visitors are invited to meet members of the Society at the Stapenhill Institute on Wednesday evenings.

DERBY AND DISTRICT AMATEUR RADIO SOCIETY Hon. Sec.: F. C. Ward, G2CVV, 5 Uplands Avenue, Littleover, Derby.

On Sunday, February 3rd, members had a race against time to make as many contacts as possible in the GSYY Trophy Contest. Three days later the Annual General Meeting was held, when amongst other things, the Society Officers

for 1963 were elected.
On February 13th members attended a
Hi-fi demonstration and all those who attended on the 16th spent an enjoyable evening at the Annual Dinner and Dance.

The last meeting in February was especially for the junior members and was devoted to a demonstration of simple

measuring equipment.

March began with a sale of surplus equipment held on the 6th.

Future Event:
March 13th—"Car Radio Interference
Problems" by R. Barrell.

LOTHIANS RADIO SOCIETY Hon. Sec.: W. T. Sutherland, GM3JWS, 47 Great King Street, Edinburgh 3.

The evening's entertainment for the meeting of February 14th took the form of a "Brains Trust". On February 28th the Rev. W. Ferrier chose "2-metre Aerials and Progation" as the subject of his lecture.

NORTHERN HEIGHTS AMATEUR RADIO SOCIETY

Hon. Sec.: A. Robinson, G3MDW, Candy Cabin, Ogden, Halifax, Yorks. The evening of February 13th was spent in an informal atmosphere with members enjoying a ragchew. On the 27th, however, G3ADG gave a formal lecture on the prob-lems of "TVI and BCI".

Future Event: March 13th—Spares sale.

PURLEY AND DISTRICT RADIO CLUB

CLUB
Hon, Sec.: E. R. Honeywood, G3GKF,
105 Whytecliffe Road, Purley, Surrey,
Early in February Mr. B. Wynn (G8TB)
gave an interesting talk entitled "Why be
Afraid of Transistors", and on the 15th a
constructional contest, which was open to
all members, was held and judged.

READING AMATEUR RADIO CLUB Hon. Sec.: R. G. Nash, G3EJA, "Peace-haven", 9 Holybrook Road, Reading, Berkshire.

The only meeting held in February was on the 23rd and was devoted to a talk and demonstration of "Transistor Gear for 160m" which was given by G3OLA.

ROTHERHAM AND DISTRICT RADIO CLUB

Hon. Sec.: M. Parkin, SI Far Lane, East Dene, Rotherham, Yorkshire.

At the recent Annual General Meeting, held at the new clubroom, a new committee of officers was elected.

SLADE RADIO SOCIETY
Hon. Sec.: D. D. S. Williams, 117 The Boulevard, Wylde
Green, Sutton Coldfield, Warwickshire.
On February 8th, members had the opportunity of airing their
views on the subjects of d.f. and the Club station, both of which
play important parts of the Society's activities. Visitors were
welcome at the Society's annual auction sale of surplus equipment,
held on February 22nd.

Entruce Event:

Future Event: March 9th-Film show.

(Continued on page 1142)

# "HAMS CAN'T LIVE ON BREAD ALONE"

THE letter received in the PRACTICAL WIRELESS offices the other day from Roger Barker was not the only one of its kind we have received within recent months. It seems as though there are a number of people around the country who, like Mr. Barker, are cager to start an amateur radio society in their own locality. This is, of course, a very laudable desire, as there are, no doubt, many amateur radio enthusiasts who still have no local club to provide for their special needs; but anyone setting out to fulfil such a desire must not underestimate the difficulties involved.

We would point out for a start, that the first essential of a radio society is not a 100W transmitter, nor a specially designed club tie, nor even a club-room, but, undeniably, it is enthusiastic members who provide the foundation of a club, and it is the degree of enthusiasm and the number of members that will decide whether the new club will prosper or die. This seemingly obvious fact is one that will easily be overlooked by anyone starting a club. Indeed, a few of the clubs who regularly send reports to P.W. are despairingly short of members, and seem in danger of petering out altogether; and in the knowledge of the fact that a few dozen more members would ensure an energetic society doing valuable work in educating youngsters in the ways of radio, we feel a deep sense of pity for those few enthusiastic people who must have existed at the inception of each of these clubs.

So for the potential founder members of radio societies, it is essential that they always strive to increase the membership, and never allow the number to drop to less than a certain minimumthe exact number becoming obvious with time-below which the club could not possibly survive.

This, then, is the prime consideration of people like Mr. Barker. Another point worthy of note, however, is that the radio enthusiast, like anyone else, needs some "side-shows" to keep his mind from becoming weary of the "main attraction". In other words, the club organiser must make sure that meetings are not always devoted entirely to radio subjects and that the social side is not neglected. It is true to say that "hams can't live on bread alone", so try to break the diet of d.f. contest and morse practice with the occasional bar-b-que or outing.

Roger Barker is only 17 years old and he is going to need a few hard-working lieutenants and many supporters to make his venture succeed and so we print his address in the hope that anyone interested will get in touch and that yet another amateur radio society will emerge: -67 Balvernie Grove, Southfields, London, S.W.18.

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1U5	5/6			30 L1	7/6	ECC82	6/9	KT33C		UCH42	9/6
3Q4	8/-	68N7G1	6/-	35 L/IG	7/6	ECC83		KT66		UF41	8/6
364	5/9	6V0G	7/6	35W4	8/6	ECC84		N17		UL41	8/6
3V4	6/6	6X4	5/-	35Z4GT	8/-	ECF30		N18	8/-	UY41	7/6
5Y3GT	5/-	6X5G	5/9	3763	7/8	ECF82		N19		W17	7/6
5 <b>Z4G</b>	7/6	787	9/6	80	6/+	ECH42		N709		W76	4/6
6AK6	6/6	8D3	4/-	DAF91	7/6	ECH81		PCC84		W142	8/6
6AL5	4/-	9D7	9/6	DAF96		ECL80		PCF80	7/6		7/6
6AM6	4/-	12AD6	11/6	DCC90	12/6	ECL82		PCF82	7/6		9/-
6AT6	6/-	12AH8	10/-	DF91	3/+	EF41		PCL82		X 150	9/-
GBA6	5/-	12AT7		DF96	8/-	EF80	8/-	PCL84		277	4/-
6BE6	7/-	12AU7	6/0	DH76	7/6	EF86		PL81		ZD17	7/6

High Stability Resistors \( \frac{1}{2}W \) 5% 50 \( \Omega \) to 1M, 9d. Midget Ceramics 500 v. 9d. Coax. Super quality \( \frac{1}{2}m \), 6d. yd. Plugs 9d. Sockets 9d. Siltoon H.T. Rects. 250v. 300 MA \( \frac{1}{2}m \), 19d. Contact Cooled 250v. 50 MA 9(6, 55 MA 9(6, 55

NEW TRANSISTORS BY MULLARD. OC19, OC26, OC86, 25/-; OC44, OC45, 9/-; OC70, OC71, 6/-; OC72, 7/6; OC72 matched in prs. 16/-; OC74, OC75, OC78, OC81, 7/6; OC82, OC170, 9/6.

#### VALVES MATCHED IN PAIRS

EL34 27/6, EL84 15/-, N709 15/-, 6V6G 15/-, 6BW6 14/- per pair. Push Pull O.P. Transformer for above 3-15 Ω 14/6, P. & P. 1/6, 12lm. P.M. Speakers 3 Ω 24/6. Baker's "Seihurst" 12lm. 15 Ω 15W, 80/-, 12lm. Stereo

#### SETS OF VALVES

EC1142, FF41, EBC41. EL41: EZ40....37/6 FCH42, UF41, UBC41, UL41, UY41....35/-UL41, UY4 C.O.D. 2/6.



# rade ews

#### 150W TRANSMITTER KIT

THE American firm of electronic kit manufacturers, Knight Kit Electronics, has recently announced a new addition to its range—the T-150 a.m./c.w. transmitter kit. This transmitter operates with 150W peak a.m./c.w. input on 80m through 10m, and 100W peak a.m./c.w. on 6m.

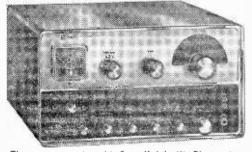
The made-up instrument features a specially designed v.f.o., which provides highly stable frequency control on all bands, and also an adjustable \( \pi\)-network output circuit that matches

40 to  $600\Omega$  aerial impedances.

Another noteworthy feature is the frequency spotting selector-switch position, which allows tuning of the transmitter before switching on the final amplifier. This offers the advantage for the operator to zero-beat an incoming signal without placing the transmitter on the air.

The exporters of Knight Kit Electronics products in Britain are Ad. Auriema Ltd., 414

Chiswick High Road, London W.4.



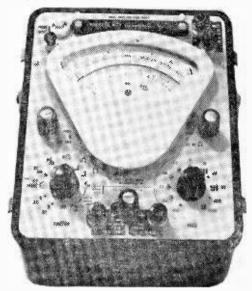
The new transmitter kit from Knight Kit Electronics.

#### TRANSISTORISED MULTIMETER

AT the recent Physical Society Exhibition, Avo Limited exhibited three of their latest developments. One of these was a transistorised multimeter which has included in its design the facility for the measurement of low a.c. and d.c.

This instrument, designed around a "chopper" amplifier having a full-scale sensitivity of 10mV, may be used for the measurement of d.c. voltage, d.c. current, a.c. voltage, a.c. current and resistance. The use of a probe enables r.f. voltages between 10mV and 4V to be measured at frequencies up to 1,000Mc/s.

One of the features of this multimeter is a "battery check" facility, included to ensure that the supply voltages do not fall below the limit required for satisfactory operation. The hermetically sealed movement has a scale length of 5in. and incorporates an anti-parallax mirror. The manufacturers of this instrument are Avo Limited, Avoset House, 92/96 Vauxhall Bridge Road, London S.W.1.



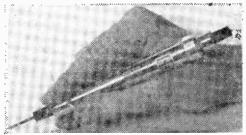
Avo Limited's transistorised multimeter.

#### HIGH GAIN SIGNAL TRACER

THE latest addition to the range of test equipment made by Controlled Electronics is a pocket-sized signal tracer, known as the 670. The complete instrument comprises a high gain signal tracer and detector.

Two plug-in input probes are provided; one for a.f. and the other for detecting modulated r.f. signals. The 670 is a useful servicing aid in all manner of circuits, for locating hum, noise and

signal breaks, etc.



The pocket-sized signal tracer made by Controlled Electronics.

The output is obtained through a miniature ear-piece, and the price of the complete instrument is £6 19s. 6d. The makers are Controlled Electronics 62 High Street, Croydon, Surrey.

#### CONTINUITY TESTER

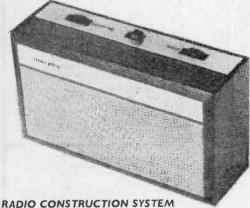
A NEW instrument, specially designed for rapid continuity checks in all electrical equipment, has been brought on to the market by M.P.E. (Finchley) Ltd. The unit is called the MPE Trantest and when used, gives an audible indication of continuity and will quickly detect such things as dry joints and the effectiveness of anodised plating on metal surfaces.

Advantages of the Trantest are that it will not

indicate continuity through inductive or capacitive impedances and that it cannot damage semi-

conductor devices.

The price of the Trantest, complete with probes, is £4 10s. and it is made by M.P.E. (Finchley) Ltd., Dollis Park, Finchley, London N.3.



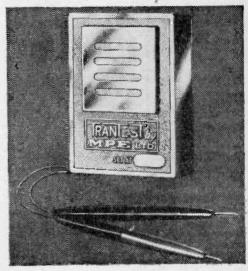
METHOD of constructing electronic circuits, in step-by-step stages, has been brought on to the market by Radionic Products Ltd.

From a simple radio receiver, the circuits progress to a six transistor set capable of receiving

long and medium wave broadcasts. All the components are attached to plastic mounts which are fixed in position on a Perspex "chassis" which is perforated with holes at regularly spaced intervals. On the other side of the chassis brass strips can be attached to join components, and in effect, act as the wiring. As the "chassis" is trans-parent, the whole circuit can easily be followed through and checked, even by a complete beginner to radio construction.

Four of these Radionic sets are available, each set varying in

complexity and price. The prices range from £6 12s. 6d. to £16 14s. 6d. and the makers are Radionic Products Ltd., Adastral House, Nutfield, Redhill, Surrev.



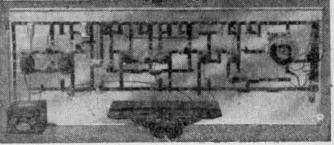
The MPE Trantest Continuity tester.

Left: A new seven-transistor receiver made by Murphy Radio Ltd.

#### 7-TRANSISTOR PORTABLE RECEIVER

A SEVEN-TRANSISTOR radio-weighing only 2lb—is the latest model to be put on to the market by Murphy Radio Limited. This receiver is the model B801 and is a portable model capable of tuning over the whole of the medium and longwave bands. Its dimensions are 64in. x 3½in. x 2in., and its price is 12½ guineas. A separate carrying case is also available at 25s.

The B&O1 is made by Murphy Radio Limited, Welwyn Garden City. Hertfordshire.



A view of a 6-transistor receiver, made up from a Radionic Kit.

CLUB NEWS (continued from page 1138) SPEN VALLEY AMATEUR RADIO SOCIETY Hon. Sec.: L. A. Metcalfe, IA Moorlands Road, Birkenshaw, Bradford, Yorkshire.

The subject of the lecture given by T. H. A. Withers, on February 7th, was "Converters, Receivers and Transmitters", and S. Marsden's talk on "What's New" was well received by his audience at the meeting on the 21st.

On March 7th, Mr. J. Belcher lectured on the subject of

"Direction Finding".
WESSEX AMATEUR RADIO GROUP
Hon. Sec.: G. J. Fowle, 138 Surrey Road, Branksome, Poole, Dorset

The Annual General Meeting was held on February 4th this year. At the meeting held on March 4th, members held a talk on "Electronics".



# TRANSISTOR RADIOS

The finest receiver at present available for home construction. Fully tunable long and medium wavebands. Uses 7 Mullard Transistors: OC44 2 OC45's. OC71 Transistors: OC44, 2 OC45's, OC71 OC81D and 2 OC81's, plus Crystal Diode

# "REALISTIC"

FEATURES

- 7 Transistor Superhet. 350 Milliwatt output into 4-inch high flux speaker.
- All components mounted on a single printed circuit board, size 5½ x 5½in. in one complete assembly.
- Plastic cabinet, with carrying handle size 7 x 10 x 3 in. in choice of colours:
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- Operates from PP9 or similar battery.
- comprehensive data supplied with each Receiver.
- All coils and I.F.'s, etc., fully wound ready for immediate assembly.



An Outstanding Receiver. Lasky's Price for the complete parcel inclu-ding Transistors, Cabinet, Speaker, ctc., and Full Construction Data:

£6.19.6 Postage and Packing 4/6 Battery 3/9 (included free with complete parcel). Data and instructions separately 2/6, refunded it you purchase the parcel.

# The SPRITE

Inclusive price of

89/6

P. & P. 3/6 extra.

★ Six-Transistor Superhet Miniature Personal Pocket Radio. ★ Tunable over Long and Medium wavebands. ★ Uses PP3 battery. Ferrite Rod acrial. ★ I.F. Frequency 470 Kcys. Transistors: 3 Philos 2067×2 Mullard OC61 M, OC81 DM and OA59 diode. ★ 3 inch speaker. ★ Printed circuit 21 x 2n. ★ Slow Motion Drive. ★ In Plastic Case.

In order to ensure perfect results, the SPRITE is supplied to you with R.F. and I.F. stages. Driver and Output stages, ready built with all components ready mounted on the printed circuit. To complete assembly you only have to fit the wavechange switch, tuning condenser and drive, volume control, earphone socket and aerial rod, the remaining components all having been prefitted at the lactory for you. The SPRITE is offered as above pre-assembled, plus cabinet, speaker and all components or final construction, at the inclusive price of 89/6. Postage and packing 3/6 extra. For the construction of the inclusive price of 89/6. Postage and packing 3/6 extra feather case with the separately. 2/6. Refunded il percol is purchased. Real call leather case with the separately and carpinone and case for earphone 10/- the lot extra. Make no mistake this is a SUPERHET receiver of genuine commercial quality. It is not a regenerative circuit.

* A 6-transistor plus 2-diode superhet receiver using the latest circuitry. * Three Mullard AFII7 alloy diffused transistors are used with OA79 and OA91 diodes, followed by OC61D and two OC61's in push-pull. * I.F. requency 470 Kc/s. * Covers the full medium and long wavebands. * Sockets provided for personal earpiece or tape recorder, and car radio aerial. * Larse internal ferrite rod aerial gives high sensitivity. * Uses four 1.5 v. pen torch batterles. * All components mounted on a single printed circuit. Simple stage by stage instructions. * Cabinet size 63 x 4 x 14 in. With carrying handle. * All colls and I.F. 's ready wound. ALL COMPONENTS AVAILABLE SEPARATELY. Dala and instructions separately 216. Refunded if you purchase the parcel.



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A complete stereo amplifier of unsurpassed quality, with inputs for radio, tape recorder. F.M. tuner or any other hi-fi source, either monaural or stereo. Output power 5 watts total (2) watts each channel). New and unused, listed at 16 rns.

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A continental manufactured 2-speed tape recorder with 11 x 3fin. 1.p.s. Twin track recording to international standards. * Takes 5fin. spools. * Fast forward and fast rewind. * Record level indicator. * Inputs for mic. radio and pick-up. For use on 110 and 200-250 v. 5 C.p.s. mains. * Disital position indicator. * Inputs for mic. radio and pick-up. Takes who case with the control of the wood case with metal to power factors who case with metal to power factors who case with metal to power factors with the control of the contr

#### KAPURA Model U1 Multi-Test Meters

★ Complete with test leads. ★ Brand new, fully guaranteed. Sensitivity: 1,000 ohms per volt A.C.

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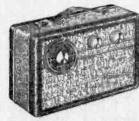


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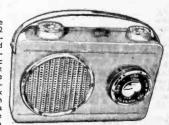
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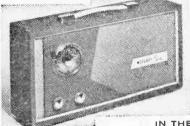
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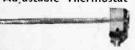
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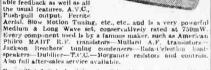


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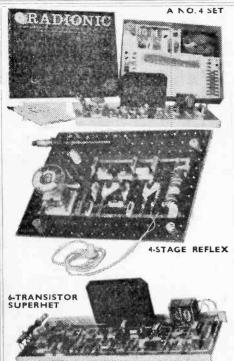
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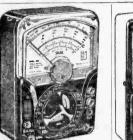
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PRACTICAL WIRELESS, APRIL, 1963

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