THE WIRELESS ENGINEER AND

EXPERIMENTAL WIRELESS

NUMBER 123 VOLUME X

DECEMBER 1933

A JOURNAL OF RADIO RESEARCH AND PROGRĘSS



PUBLISHED BY ILIFFE & SONS LTD. DORSET HOUSE STAMFORD STREET LONDON S.E.1

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 A Symmetrically Opening Slit. By A. Elliott, Ph.D., D.Sc.
 NEW INSTRUMENT:
 A Modified Sherrington Stethograph. By J. R. Bell and A. R. Smallie.
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 A Bridge for Small Inductances. By A. T. Starr, M.A., B.Sc.
 On the Suppression of Hermonics of the Einthoven String

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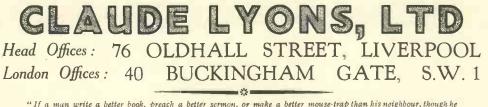
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A Journal of Radio Research & Progress

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EDITORIAL.

Technical Editor Prof. G. W. O. HOWE D.Sc., M.I.E.E.

VOL. X. No. 123

DECEMBER 1933

C O N T E N T S

HIGH POWER PENTODE AS AN ELECTRON COUPLED TRANSMITTER. By J. C. W. Drabble and R. A. Yeo, B.Sc. CIRCLE DIAGRAMS OF VALVE INPUT ADMITTANCE AND

AMPLIFICATION FACTOR. By F. M. Colebrook, B.Sc., D.I.C., A.C.G.I.

NAVAL Addre	WIRELESS,	I.E.E.	Wireless	Section,	Chairman's	662
CORRESE	PONDENCE					663

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GENERAL INDEX TO ARTICLES, AUTHORS AND ABSTRACTS IN VOLUME X, JANUARY-DECEMBER, 1933

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648

665

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VOL. X.

DECEMBER, 1933.

No. 123

Editorial

Electrical Interference with Broadcast Reception

BOUT six months ago the Institution of Electrical Engineers appointed a committee to inquire into the subject of Electrical Interference with Broadcasting, and some of the sub-committees of this committee have recently issued a preliminary report. Our readers will be interested in the parallel activities of the "Kom-mission für Rundfunkstörungen" set up by the Verband Deutscher Elektrotechniker. This committee has, through two of its sub-committees, issued two draft regulations, which were published in the E.T.Z. of 28th September, with the request that any objections should be lodged with the V.D.E. before 30th November. These draft regulations cover six pages of the E.T.Z., and go into considerable detail. The first draft deals with the precautions to be taken in lines and networks, and in the receiving set and aerial; the second, which is much longer, deals with the steps to be taken to render electrical apparatus non-disturbing. In each case there is a preliminary statement that the regulations are intended to indicate how, in the present state of the art, interference can be reduced, with due regard to price, practicability and reliability. The draft dealing with networks is subdivided into four sections dealing respectively with power networks, trolley wires, signalling networks and the radio receiving apparatus

itself. In the case of power networks it recommends that all straight-through and tee connectors should be firmly secured, that all contact with tree branches, straw, etc., should be avoided, as should also all sharp points on high voltage wires, clamps, etc. That insulators should be kept clean and replaced if damaged, and that the lines should be run underground wherever possible, especially in thickly populated districts. It recommends that the aerial should be erected as remote as possible from the wiring system of the premises. In connection with trams it points out the necessity of good mechanical construction of the collecting wheel or bow so as to maintain steady pressure and contact, and also the use of materials which do not tend to spark production. It also emphasises the importance of maintaining the overhead wire and the track in good condition in order to avoid sudden blows on the collector with consequent vibration and intermittent contact. A further point is the necessity for maintaining good conductivity at the rails joints to prevent the flow of high-frequency currents through the earth. The recommendations for signalling networks are almost identical with those for low-voltage power networks. For aerials it is recommended that they be as high as possible and kept as far as possible from the house and any disturbing wiring;

it is also suggested that the lower part external circuit from disturbances arising may be screened and in some cases the at the commutator. Further protection screen used as a counter-capacity instead of , is then obtained by connecting condensers

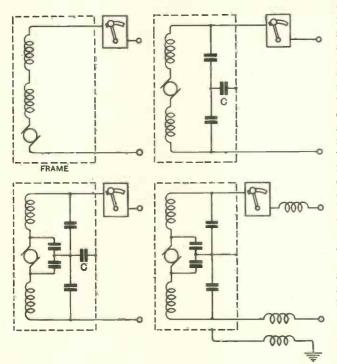


Fig. 1 --- If the frame is earthed, the condenser C is replaced by a direct connection.

employing an earth connection. If an earth connection is used, it should be as short as possible, and not parallel to interfering leads. Little is said about the receiving set beyond suggesting screening and the insertion of filters in the supply leads.

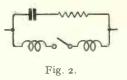
The second draft dealing with the steps to be taken to render electrical machines and apparatus innocuous gives a great many diagrams showing how the condensers and choke coils may be connected. It is emphasised that the condensers and coils must be so constructed that they do not decrease the efficiency or the reliability of the apparatus to which they are fitted. Special stress is laid upon the importance in all new construction of the symmetrical distribution of the field windings with respect to the armature. If in a series motor the field winding is divided into two parts with the armature connected between them, they will serve as chokes and protect the

of about 0.1 μ F across the whole machine and, if this proves insufficient, other such condensers across the armature. Finally, if all these prove insufficient, choking coils should be inserted in the supply wires. In all the diagrams the steps are numbered in the order in which they should be applied. Diagrams are given for series and shunt motors, motors with commutating poles and for rotary converters. If the frame of the machine is not earthed, a condenser should be connected between it and some point of the winding to provide a path for high-frequency currents. As an example of the successive application of protective devices diagrams are given for a series motor. As a final step a choking coil is even inserted in the earthing lead from the frame of the motor.

It is suggested that switches need only be considered when they are operated very frequently. If the switch arcs on break it causes little interference, but if it only sparks it is much more troublesome

and should be shunted with a condenser; if necessary, a damping resistance should be inserted in series with the condenser. Still further protection is obtained by inserting choke coils on either side of the switch as shown in Fig. 2. This applies also to signalling apparatus in which contacts are made and broken. It is stated that the values of the condensers lie between o.I and

2.0 μ F and of the resistances between 5 and 500 ohms, the best values being determined by experiment in each case. In the case of electric bells



the contact should be connected between the windings of the two magnet cores, in addition to being shunted by a condenser and resistance. In extreme cases, choking coils may have to be inserted in the leads and a condenser connected across them as in the series motor. Somewhat similar precautions should be employed with vibrating contact rectifiers.

Special arrangements are necessary with rotary rectifiers for supplying X-ray and dust depositing plant. High resistances or choke coils of low capacity should be inserted in the leads from the contacts, in addition to filters on the primary side of the transformer. Filters should also be fitted to the primary side of the filament-heating transformer for hot cathode X-ray tubes. If these precautions are insufficient the whole apparatus should be metallically screened in a Faradav cage. It is stated that large mercury rectifier plants do not as a rule cause any disturbance, but that in small ones condensers should be connected between the cathode and the anodes, and, if necessary, high-frequency chokes inserted in the anode leads between the anodes and the condenser tappings. The same applies to any form of gaseous rectifier. In the case of Tesla coil medical apparatus, filters should be inserted between the apparatus and the mains, and the open oscillatory circuit should be " closed " by bringing out a connection from the other terminal of the Tesla coil-if necessary, through a condenser-and using it to screen the working electrode.

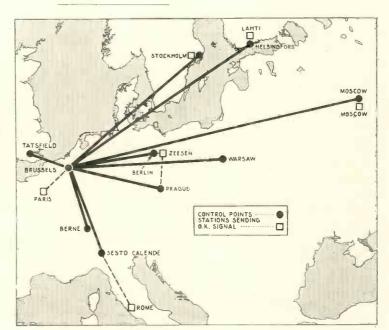
Diathermy apparatus is very troublesome, and a filter of several sections should be inserted in the supply wires and kept remote from the high-frequency apparatus and operating leads. If necessary, the high frequency part of the apparatus, including the patient, should be enclosed in a metallic screen.

It is pointed out that radio-receiving sets may themselves be the source of interference, not only due to the well-known oscillations set up by excessive back-coupling, but also due to faulty connections in the set or aerial and contact between the aerial and surrounding bodies. It is stated that the latter can cause wide-reaching interference. It is also stated that excessive back-coupling may cause interference in neighbouring receivers even if it is not carried to the point of oscillation. Another cause of interference is the modulation at the supply frequency of the carrier frequency picked up by the supply leads and passed into the rectifier unit.

What legal force, if any, will be given to these regulations when they have been approved we do not know, but they will certainly be useful to any other body, such as our own Institution of Electrical Engineers, which is considering this important question. G. W. O. H.

Lucerne Wavelength Plan

T 11 p.m. on 14th January all European broadcasting stations will close down. Then, one by one, in each of seven main groups, they will resume transmission according to special schedules, their new wavelengths being checked at the control points shown in the map. Certain high-power stations, also shown, will broadcast the results of each calibration. The centre of operations will be the Brussels checking station of the International Broadcasting Union.



High Power Pentode as an Electron Coupled Transmitter*

By J. C. W. Drabble and R. A. Yeo, B.Sc.

SUMMARY.—Experiments on electron coupled transmitters, using a silica pentode capable of dealing with an input of 4 kW. are described. Conditions for most efficient working are obtained. Both efficiencies and stability are comparable with those of a two-stage master oscillator transmitter. A method of modulating this pentode is investigated and it is found that it would be possible to modulate this 4 kW. pentode by means of a small receiving valve and transformer. The short wave limitations are discussed and found to be about 15 metres.

Introduction

CERTAIN amount of work has been done by Lt. J. B. Dow† in America on electron coupled oscillators, that is, oscillators in which the coupling to the output or load circuit is provided by the electron stream reaching the anode of a four-electrode or screen grid valve, the output circuit being connected to the anode and the oscillatory circuit to the two grids of such a valve. This type of circuit has certain disadvantages, the two most important being :-

(1) The proximity of a high potential screen to the anode gives rise to secondary emission effects which are likely to cause considerable trouble.

(2) In order to prevent feed back from the driven to the driver circuit through the anode-screen capacity neutralisation is necessary unless an inverted type of circuit in which the screen is at zero high frequency potential is used.

Preliminary Experiments

The following investigation employing a pentode as an electron coupled oscillator was suggested from consideration of the fact that the earthed or suppressor grid of such a valve would act as an electrostatic screen and make neutralising unnecessary and secondary emission impossible. The work was started before it became known that Lt. Dow had continued his research, using the pentode, but so far as is known none of his results in that connection has yet been published.

The circuit used for the greater part of these experiments is shown in Fig. 1, where it will be seen that the driver circuit is of the Hartley type and is connected between the first and second grids, the output circuit being connected between anode and filament.

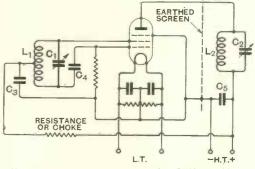


Fig. 1.—Pentode connections for C.W. working.

In the original experiments small receiving pentodes were used. Very promising re-sults were obtained using a Marconi PT2, a two-volt pentode which works with a maximum potential of 150 volts on screen and anode when used as an output receiving valve. In these tests the potential used was never increased beyond 100 volts on both anode and screen.

With the driver circuit oscillating at a wavelength of 80 metres (3.75 megacycles/ sec.) it was noticed that considerable changes in the applied H.T. voltage and in the tuning of the output circuit could be made without seriously affecting the generated frequency of the driver circuit. A 28 per cent. change in H.T. caused a change of 100 cycles/sec. in the driver frequency, representing a frequency change of one part in 37,500. Con-

^{*} MS. received by the Editor August, 1933. † "A Recent Development in Vacuum Tube Oscillator Circuits."—J. B. Dow, *Proc. I.R.E.*, December, 1931. "Electron Coupled Oscillator Circuits."—J. B. Dow, *Q.S.T.*, January, 1932.

siderable changes in output tuning were made without causing a greater change than 500 cycles/sec. in the master frequency. It was noticed with these small receiving pentodes placed at right angles to each other, but no screening was used. This precaution would possibly have given still further improvement to the frequency stability and possibly

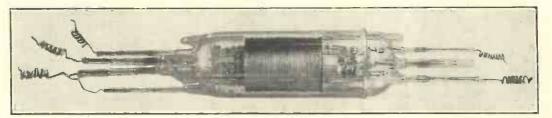
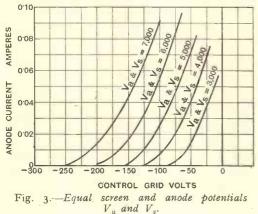


Fig. 2.—Silica Pentode constructed in H.M. Signal School, Portsmouth.

that the optimum value of the grid leak was somewhat critical, for the PT2 being about 5,000 ohms. The Mullard PM22 would not work satisfactorily with this value of grid leak, but the investigation was not pursued to any extent with these valves as it was desired to proceed to high power as soon as it was ascertained that the circuit functioned as anticipated. A rough comparison was carried out with 100 volts H.T. between the pentode circuit using a PT2 and a twostage master oscillator transmitter using PM202 valves both as master and output. The efficiency of the pentode circuit appeared to be slightly less but the frequency stability slightly better than the two-stage transmitter.

It should be understood that these tests were only considered to be in the nature of preliminary experiments and no elaborate precautions were taken to obtain the best working conditions with these small valves. The input and output circuits were arranged as far apart as practicable and the coils



to the efficiency. The use of one of the more recent screened pentodes in which the anode is brought out to a terminal on the top of the envelope offers further possibilities for improved working owing to the absence of capacity between screen and anode leads in the pinch.

The work with the small receiving pentodes appeared to be so promising that it was decided to proceed to high power experiments with the largest pentode available.

Description of Silica Pentode

This valve which was constructed in H.M. Signal School, Portsmouth, is illustrated in Fig. 2. The envelope is made of transparent fused silica and is 10 cms. in diameter and 32 cms. in length. Including seals, the overall length of the valve is 60 cms. All seals are of the lead plug type with molybdenum rods as internal conductors and flexible stranded copper external conductors.

The anode and high tension screen seals are brought out at one end, and suppressor screen, grid and both filament seals at the other.

The filament is a loop of pure tungsten wire kept in tension by a spring and has a total length of 30 cms. and diameter of 0.7 mm. This requires a heating current of 28 amps. at 15 volts. The dimensions of the other electrodes which are cylindrical in form are as follows :---

		Diameter	Length.
Electrode.		in cms.	in cms.
Control grid	• 2	3.0	16
H.T. screen	A .A	4.5	18.5
Suppressor screen	5 x	6.0	14.0
Anode	- <mark>-</mark>	8.0	I2.0
	•		В

The three grid structures are built of molybdenum wire, 0.15 mm. diameter, in a 1.5 mm. mesh construction. The anode is made of molybdenum strip wound basket fashion to a cylinder of the size given. During bombardment the control grid was joined to filament and a power of 4.8kW. was dissipated by the other electrodes which were all joined together and to the high tension supply.

This valve was not designed for the purpose outlined in these experiments, having, in fact, several disadvantages from that point of view, the two most important being :—

(a) The H.T. and suppressor screens have a closer mesh construction than is This will be seen by reference desirable. to the static characteristics of the valve which are shown in Figs. 3, 4 and 5. These reveal the fact that with equal potentials on anode and screen, the screen current is in general greater than the anode current. Thus, when this valve is used as an electron coupled oscillator, the driver portion absorbs an unnecessarily large proportion of the total input and so reduces the overall efficiency. These facts are all confirmed in the subsequent experimental work.

(b) In order to obtain the greatest amount of screening between driver and driven circuits, the anode seal should be brought out at one end, all the remaining seals being brought out at the other. In addition to allowing considerable improvements in screening, it would also be possible to obtain a better circuit lay-out of the driver circuit, a point which is of considerable importance when it is desired to work at short wavelengths.

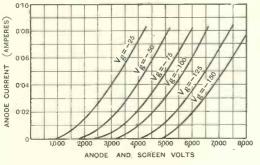
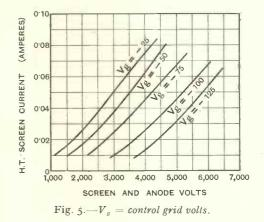


Fig. 4.— $V_q = control grid volts$.

Optimum Load

In order to obtain accurate figures for the efficiency of this valve, preliminary tests were carried out to ascertain the optimum load impedance for the output circuit. A



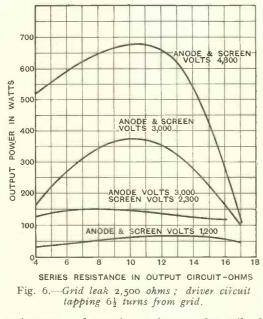
Hartley circuit consisting of 15 turns of ³/₈-inch copper tubing on a 5-inch former and 100 $\mu\mu$ F. variable condenser set at maximum was connected between grid and H.T. screen, and this including valve capacities tuned to 80 metres. The output circuit consisted of 9 turns of $\frac{3}{6}$ -inch copper tubing on an 8-inch former and a 100 $\mu\mu$ F. variable condenser. With the latter set at 77 $\mu\mu$ F. this circuit also tuned to 80 metres. A series of readings of input and output power were taken, the variations being made by connecting various values of resistance in the tuned output circuit. These readings are shown plotted in Fig. 6 and indicate that for the circuit used the best output is obtained with a resistance of the order of 9–12 ohms in the output circuit. This corresponds to an output load impedance of from 15,000 to 20,000 ohms taking into account anodescreen capacity in parallel with the tuning capacity, but it will be seen that the value is not very critical. This estimate of optimum anode load impedance was made for three values of applied voltage, both anode and screen potentials being the same. Another estimate of optimum load impedance was made with the screen at a lower potential than the anode. With 3,000 volts on the anode and 2,300 on the screen, the optimum load impedance does not change very considerably, having a slightly higher value.

In this case, the lower screen potential was obtained by inserting a resistance in the H.T. lead from the common supply. It may be mentioned here that it was found necessary to insert a high frequency choke or a resistance of at least 1,000 ohms in this lead in order to eliminate coupling between driver and driven circuits *via* the common H.T. supply; if this was not done, the two circuits combined to form an inefficient oscillatory circuit of longer wavelength than that to which either was tuned.

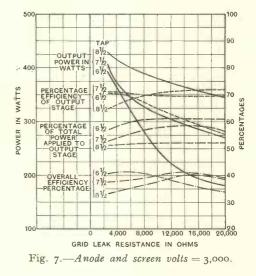
In all of the subsequent tests on 80 metres (except those on frequency stability), the series high frequency resistance of the output tuned circuit was 9 ohms, a value which was checked in a separate experiment. This is equivalent to a load impedance of about 20,000 ohms and it will be seen that this represents a load fairly near the optimum for most conditions under which the valve was subsequently operated.

Optimum Conditions for the Driver Circuit

The next set of readings was taken in order to determine the best value of grid leak



resistance and tapping point on the coil of the driver circuit. The anode and screen volts were kept constant at 3,000. Curves plotted from the readings taken are shown in Fig. 7. In determining the best working conditions of the circuit, it is necessary to take into consideration the four factors: output, watts, overall efficiency, efficiency of the output stage, and the ratio of input power to anode stage over total power input. This last factor is of some considerable importance in a circuit of this nature as it



gives some indication of the percentage power which is dissipated by the screen which forms the anode of the master circuit. It is quite obvious that as this is of mesh construction, the amount of power which is dissipated by it should be as low as possible and hence the ratio of input power to anode stage to total power input should be as high as possible. This applies more especially to the valve used in these experiments since the H.T. screen was not intended to dissipate a very large proportion of the input. A valve designed for an electron coupled transmitter should have a much more robust H.T. screen built up of thicker wire. On the other hand, the high values reached for the efficiency of the output stage indicate that, if necessary, the anode could be of a much lighter construction than that used, since it is not called upon to dissipate a very large proportion of the input power.

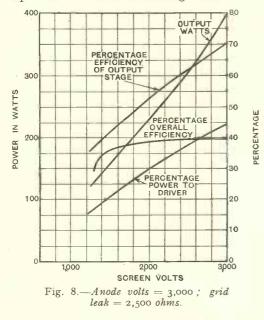
Taking all of the factors into consideration, it will be seen that the best conditions are obtained with a grid leak value of the order of 2,500 ohms and with a tapping on the driver circuit about $6\frac{1}{2}$ turns from the grid end. With these conditions, the overall

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December, 1933

efficiency is just over 40 per cent. and the efficiency of the output stage just over These efficiencies are com-70 per cent. parable with those of a two-stage master oscillator transmitting on this frequency, that of the output circuit having reached almost the maximum efficiency of a class B The percentage of the amplifier stage. input power which is absorbed in the driver stage is of the order of 40 per cent. so that it may be assumed that the screen forming the anode of the driver stage is called upon to dissipate not more than 25 per cent. of the total input. The H.T. screen in this valve is just capable of dissipating this proportion of the total input at full load input of 4 kW. With a valve having H.T. and suppressor screens of more open mesh, the proportion of power dissipated by the screen could be reduced considerably and the overall efficiency increased.

It is interesting to note from the curves that as the tapping on the master circuit is moved away from the grid, that is, as the excitation is increased, the maximum value of overall efficiency is obtained with higher values of grid leak. This is what one would expect with a triode oscillating valve.



In order to determine the influence of screen voltage on power output and efficiencies, a set of readings was taken and are shown plotted in Fig. 8. It will be noticed that all of the curves have a rising characteristic although the overall efficiency curve flattens out after the screen volts exceed

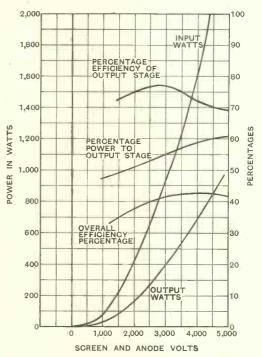


Fig. 9.—Grid leak 2,500 ohms; driver circuit tapping $6\frac{1}{2}$ turns from grid.

50 per cent. of the anode volts. It is interesting to notice that the output watts rise as the anode volts are raised relatively to the screen volts, and at this point the overall efficiency is also at a maximum. Although the percentage of power absorbed in the driver rises with rise in screen volts, this is counterbalanced by the rise in efficiency of the output stage.

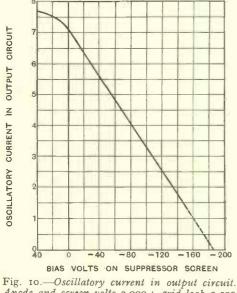
Efficiency when Working with Optimum Conditions

With the valve working with the complete set of optimum conditions as determined in the previous experiments, that is, driver tapping point $6\frac{1}{2}$ turns from the grid, grid leak resistance 2,500 ohms, output load impedance 20,000 ohms and equal voltages on screen and anode, a set of readings was taken to show the variation of efficiency and output with variation of anode and

These curves are shown in screen volts. Fig. 9. The efficiency remains fairly constant at a value just above 40 per cent. when the voltage exceeds 3,000. The efficiency of the output stage reaches the very high value of 77 per cent. at about 3,000 volts potential, but falls off slightly beyond this value. These experiments were carried out in a laboratory fitted with a limited power supply which fixed the upper limit of supply voltage to the valve at about 5,000 volts. It is considered, however, that this voltage could be increased to 6,000 without exceeding the maximum load which the valve is capable of withstanding. The output power would then be about 1.6 kW.

Frequency Stability

Measurements of frequency stability were made at a wavelength of 80 metres. The ratio L/C of the output circuit was reduced considerably for this experiment in order that finer variations of tuning could be made. The constants used were C (including anode-screen capacity) 347 $\mu\mu$ F., $L = 5.2 \mu$ H.



Anode and screen volts 3,000; grid leak 2,500 ohms.

The high frequency resistance of this circuit was such that the anode load impedance was very near optimum value. The tuning capacity of the output circuit was decreased to $306 \ \mu\mu$ F. and a change in frequency of 1,000 cycles was observed. An increase in capacity from the tuning point to $388 \ \mu\mu$ F. gave the same change of frequency. Thus a variation of about 12 per cent. on either side of the tuning capacity caused a change of about 0.025 per cent. in the generated frequency. Even with the worst weather conditions, the change of aerial capacity in a ship, due to roll and wind, would never attain this high value.

A variation in H.T. from 1,200 to 4,800 caused a frequency change of not more than 1,000 cycles, the change being in the sense of an increase in frequency for an increase in voltage. This represents a frequency change of one part in 3,750 when the H.T. voltage is varied in the ratio of 1 to 4.

The filament volts were varied one volt on either side of the working voltage, the total change of frequency observed being about 1,500 cycles in the sense of an increase in frequency for a decrease in filament volts.

If the supplies for H.T. and filament were obtained from the same machine, the frequency changes due to variation of these voltages would, to some extent, cancel each other.

Modulation

During the preceding experiments, the suppressor screen was connected to the mid point of an equalising network of resistance and capacity connected across the filament of the valve. Using the original output circuit having an equivalent impedance of 20,000 ohms, a set of readings was taken to determine the relation between a bias voltage applied to this screen and the oscillatory current in the output circuit, the anode and screen potentials being maintained at 3,000 volts. The bias battery was shunted by a fixed condenser. Curves plotted from the readings taken are shown in Fig. 10. Between 0 and - 185 volts bias, the oscillatory current bears a linear relation with bias volts. When the bias volts are increased in a positive direction, the curve begins to bend over. Thus, with 3,000 anode and screen volts and a fixed bias of about - 90 volts, distortionless modulation for I.C.W. or speech transmission could be obtained with a 100 per cent. modulation, by applying an alternating voltage of 90 volts peak value to the suppressor screen. It will be observed that the required modulating voltage is a very small proportion of the anode potential and at this point of the investigation, it appeared that a very small valve of the receiving

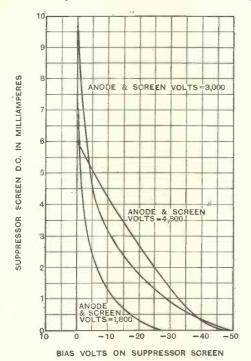


Fig. 11.—Grid leak 2,500 ohms; driver circuit tapping 6½ turns from grid.

general purpose type with its associated transformer would supply the voltage swing necessary to modulate completely this 4 kW. pentode. Before, however, coming to any hasty conclusions, it was considered advisable to ascertain whether any direct current flowed between suppressor screen and filament when the former was at a negative potential with respect to the latter. Readings were taken with three values of anode potential and the curves are shown plotted in Fig. 11. Here it will be seen that the greatest current at zero bias volts was 9.5 m.a. and this was obtained with an anode and screen potential of 3,000 volts. With the higher potential of 4,800 volts, the current at zero bias volts is less; it is also less with 1,800 volts. To check these readings a curve was plotted to show the relation between anode and screen volts and suppressor screen current with zero bias volts.

This curve is shown in Fig. 12 and confirms the results shown in Fig. 11. These curves indicate that a certain amount of power will be absorbed by the suppressor screen when a modulation is applied to it though undistorted modulation of the transmitter still lies within the capabilities of a small receiving valve, possibly of the power type. The fact, however, that the screen did take current when at a negative potential, required some explanation. It was at first thought possible that an electron oscillation of the Barkhausen-Kurz type was being produced. To test for this, the suppressor screen was connected to the filament via a pair of Lecher leads bridged by a movable thermo ammeter. A reading was obtained in the ammeter which varied with the anode potential up to 3.5 amps. at 4,800 volts, but this reading did not vary with the position of the ammeter on the Lecher leads: The wavelength of the current in this circuit was measured and found to be 80 metres and is, of course, the capacity current fed from the driver and driven circuits via the inter-electrode capacities. It was decided that electron oscillations were not present,

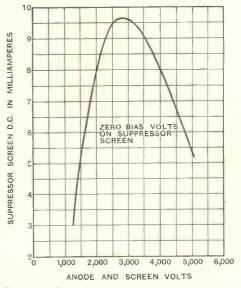


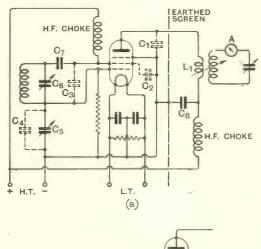
Fig. 12.—Zero bias volts on suppressor screen; grid leak 2,500 ohms; driver circuit tapping $6\frac{1}{2}$ turns from grid.

the current taken by the suppressor grid being accounted for by the fact that the large capacity current from the main circuits

EXPERIMENTAL WIRELESS

will run this electrode positive during some part of the cycle if any impedance is present in the path from suppressor grid to filament. In the case of the silica valve this path is inevitably somewhat long owing to the length of seals.

The shape of the curve in Fig. 12 cannot be at present explained.



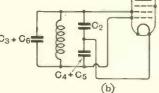


Fig. 13.—Inter-electrode capacities shown at C_1, C_2, C_3, C_4 .

At the conclusion of these modulation tests, an observation of frequency stability was made for a change of bias volts on the suppressor grid. The bias voltage was varied from 0 to -150 and no change of generated frequency was observed. Thus, amplitude modulation performed by this method would be entirely free from frequency modulation.

Lower Wavelength Limit

An attempt was made to determine the lower wavelength limit at which this circuit would operate satisfactorily. It soon became obvious that with a Hartley circuit as the driver circuit, the large interelectrode capacities rendered it impossible to obtain satisfactory operation below about 25 metres.

It will be appreciated that the capacity between the suppressor screen and the H.T. screen forming the anode of the driver circuit, which is for this valve about 20 cms., unbalances the driver circuit when the tuning capacity is small. In order to avoid this difficulty, the circuit was changed to that shown in Fig. 13a. In this arrangement, the driver circuit is of the Colpitts type requiring no tap on the coil. The circuit can be redrawn as shown in Fig. 13b and it will be seen that the correct tapping is obtained by adjustment of C_5 . The output circuit was also modified as shown in Fig. 13a, L_1 being a single turn coil of lower impedance than C_1 . With this arrangement the transmitter worked satisfactorily down to 15 metres. Owing to the inevitably large interelectrode capacities in a pentode of this size, it would be impossible to obtain a sufficiently large ratio

of $\frac{Z}{C}$ for the driver circuit below this wave-

length. Frequency doubling was tried but the overall efficiencies were so low, of the order of 5 per cent., that experiments were not pursued in this direction.

Conclusions

I. As a method of securing frequency stability, this pentode circuit compares favourably with a two-stage master controlled transmitter.

The ratio input to the driver circuit 2. to total input is undoubtedly higher than in the case where two separate valves are used, reaching values of about 45 per cent. for conditions of optimum output. Owing, however, to the high efficiency of the output circuit, which in some cases reaches a value of 77 per cent., an overall efficiency of 40 per cent. or over can be easily obtained. It is probable that a valve designed without the disadvantages mentioned in the description, that is, with screens of more open mesh, the proportion of power absorbed in the driver could be reduced and the overall efficiency increased.

3. The highest values of efficiency are obtained with low values of grid leak, the driver circuit coil tapped near the centre, and the same voltage applied to both anode and screen.

4. Distortionless modulation up to 100

per cent. for I.C.W. or speech transmissions can be carried out with small expenditure of power and complete absence of frequencymodulation.

5. For short wave working, the Colpitts circuit offers certain advantages over any other type of circuit, when used with the pentode as an electron coupled transmitter. Smaller valves having lower interelectrode capacity would enable shorter wavelengths than 15 metres to be reached. In this connection, a small pentode of the 500-volt type now available on the market, might find considerable applications among amateur transmitters and others who desire to construct one-valve master controlled transmitters, if valve manufacturers could fetch the suppressor grid out to a separate terminal or pin. A valve of this type could most probably be completely modulated direct from a microphone transformer.

The experimental work on which this article is based has been carried out at H.M. Signal School, Portsmouth, and the article is published with the permission of H.M. Board of Admiralty.

Book Review

Elements of Engineering Acoustics.

By Dr. L. E. C. Hughes. Pp. 159. Ernest Benn, Ltd., 154, Fleet Street, E.C.4. 1933. Price 8s. 6d.

Gramophones, broadcasting, and talking pictures mark the culmination of various stages of development in methods of simultaneously addressing large numbers of people, and in all these stages enormous popular interest has been aroused both on the part of the inventor and the listener. As an almost inevitable result the earnest student has been inadequately catered for and, in default of serious treatment of the subject at the Universities, he has suffered from piecemeal presentations of the more spectacular items in popular journals.

This defect has now been remedied to some extent by the institution of a Course in Electrical Communication at the City and Guilds Engineering College. The neglected child of Physics and Engineering has thus attained to adult dignity worthy of being recognised by the University of London. In the volume under review the elements of the subject of Engineering Acoustics are given by Dr. Hughes, who is Lecturer in the Course referred to, and it is refreshing to find an account of the fundamental principles stripped of the complexities which accrue in the actual design of a system containing a microphone, an amplifier, and a reproducer.

Considerable space is devoted to methods of measuring the gains and losses in the various links of the chain and attention is frequently drawn to the necessity of adhering to a logical system in such measurements. Thus the power level at any stage in an amplifier must be measured when the amplifier is properly terminated with an impedance equal to the impedance of the output load. Also the sound output of a telephone receiver is only of interest when the receiver is held against an artificial ear; results obtained when the receiver is held in open air are valueless.

In quantitative measurements the condenser transmitter is a most useful sub-standard for the calibration of microphones and reproducers. Calibration over a range of frequency at a low power level is not sufficient since amplitude and frequency distortions may arise at higher levels. Thus the amplitude distortion of an average telephone transmitter, as shown by the curve on p. 83, rises so rapidly with speech level that it is easy to see why little is gained in intelligibility by speaking loudly.

A novel conception appears in p. 11 in the use of the term acoustic-vatio to express the gain in decibels of the direct intensity of a sound over the reverberant intensity due to echoes from the walls and contents of a room. When this ratio is high the sound is hard, when low it is mellow. In the studio the acoustic-ratio is affected by room reverberation and by the directional variation in pick-up of the microphone, while in the auditorium the factors are reverberation and the concentration of high frequencies along the axis of the loud-speaker. The combination of these factors may give the same result as if the listener were placed very close to the source of sound so that the sound is extremely hard for high frequencies but not for lower frequencies—a subtle departure from fidelity which the author calls *acoustic-distortion*. The effect is so serious in talking pictures that the beam effect must

be eliminated by pointing the horns towards a wall. Another useful conception is that of *surface-loudness*, akin to surface-brightness in optics. It is the emission per unit area of the source and is large in speech but small in orchestral music. Hence when an orchestra is reproduced by a small loud-speaker the surface-brightness is excessive and the listener suffers from *sound-dazzle*.

The fundamental ideas, with which the author says he is primarily concerned rather than with formulæ, are clearly expressed and the anatomy of the subject is boldly shown without too much fleshy padding. Nevertheless, the condensation seems excessive and one would welcome larger type, more headlines, an appendix devoted to definitions with numerical examples, and a general expansion in treatment. In the second edition which will undoubtedly soon be called for, this book, which is probably destined to be the standard treatise on Engineering Acoustics, might well incorporate such features to the advantage of its readers. R.T.B.

"The Tilt of Radio Waves and Their Penetration into the Earth," editorial, *The Wireless Engineer*, November, 1933. In the last line of the left-hand column on page 591 "last line but one" should read "last line but two."

Circle Diagrams of Valve Input Admittance and Amplification Factor*

By F. M. Colebrook, B.Sc., D.I.C., A.C.G.I.

1. Object and Scope of the Paper

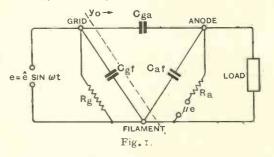
TN a previous paper¹ the writer has given a generalised analysis of valve inputadmittance and voltage-amplification. A recent re-examination of the matter has shown that in certain cases of particular practical interest the variation of both these quantities can be shown very simply on circle diagrams, which have the advantage of clear physical interpretation and which enable the most important features of the variation to be formulated without elaborate calculation.² The particular cases concerned include all those in which the variation of the anode-circuit impedance, with tuning or with frequency, can be represented as that of a constant resistance in parallel with a variable reactance. Examples are tuned anode circuit or tuned-transformer amplifying stages, and audio-frequency intervalve coupling transformers. The object of the present paper is to call attention to the circle diagrams for amplification and input admittance for such cases both for audio and radio frequencies, and to demonstrate by this means the more important practical conclusions.

The discussion applies principally to triode valves, but is equally applicable to screengrid valves in so far as conditions of operation are such as to give approximate validity to an assumption of constant mutual conductance and internal resistance.

2. The Triode Valve Equivalent Network

The network considered is illustrated in Fig. 1. Though twelve years have elapsed since this equivalent circuit was originally published and discussed by Miller in his

classical paper in the Bull. of the Bureau of Standards (Vol. 15, p. 367), no reason has been found to modify it in any essential respect. Hartshorn has shown³ that the interelectrode capacities have appreciable power-factors and also⁴ that they will vary somewhat with the space-charge conditions of the valve. Both of these factors can be allowed for if desired, but the gain in quantitative accuracy is hardly worth the additional complication of the analysis. The equivalence of the network is admittedly approximate, since some of the quantities assumed to be constant are not quite constant in fact, but the network is nevertheless very valuable as a practical simplification of an otherwise very complicated system and is justified by the results obtained.



The total input admittance will contain terms due to the actual grid-filament capacity C_{gf} , and actual grid-filament resistance R_{g} , due to grid-filament convection current, if any, or perhaps to an actual grid-leak. There will be in addition an effective admittance due to the so-called "Miller effect," arising from the action of the grid-anode capacity. The paper is concerned with the last only of these components. As a further simplification, the anode-filament capacity C_{af} will be considered as associated with the anode circuit load, and will not be explicitly referred to as a separate component.

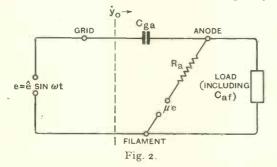
^{*} MS. received by the Editor, December, 1932.

¹ "A Generalised Analysis of the Triode Valve Equivalent Network," *J.I.E.E.*, 1929, Vol. 67, p. 157. ² Since the present article was written the author has come across a similar development of input admittance in terms of circle diagrams, by Y. Watanabe (selected papers from the J.I.E.E., Japan, No. 21, Dec., 1928). Watanabe has confirmed the theory by measurement at 100 kc/s.

³ Proc. Phys. Soc., London, 1926-7, Vol. 39, p. 108.

⁴ Wireless Engineer, 1931, Vol. 8, p. 413.

The network is thus reduced to the somewhat simpler diagram of Fig. 2. It will be sufficient to remember that the actual input admittance of C_{uf} and R_g must be added to the effective input admittance of the system to the right of the line \dot{y}_0 as shown in Fig. 2, and that the admittance of the anode-filament capacity



must be added to that of the actual anode circuit load. With this understanding the input admittance \dot{y}_0 will be written in the form

$$\dot{y}_0 = G_0 + jS_0$$

and the anode circuit load admittance as

$$\dot{y} = G + jS$$

The valve a.c. conductance will be written as $G_a = \mathbf{I}/R_a$, the amplification factor as μ , and the mutual conductance μG_a will be written as g. The input e.m.f. is considered to be a maintained e.m.f. $e = \hat{e} \sin \omega t$, represented by the vector e, and the voltage amplification v/e is represented by the operator \dot{m} .

3. Operational Expressions for Amplification and Input Admittance

The circuit analysis is quite straightforward and is given in the earlier paper. The results are

$$\dot{y}_{0} = \left(\frac{g+G_{a}+\dot{y}}{G_{a}+j\omega C_{ga}+\dot{y}}\right)j\omega C_{ga} \quad .$$
 (I)

$$\dot{m} = \frac{j\omega C_{ga} - g}{G_a + j\omega C_{ga} + \dot{y}} \qquad \dots \qquad (2)$$

Separation of \dot{y}_0 gives

$$G_{0} = \frac{\omega C_{ga}(G_{a} + G + g) + gS}{(G_{a} + G)^{2} + (S + \omega C_{ga})^{2}} \omega C_{ga} \qquad (3)$$

$$S_{0} = \frac{(G_{a} + G)(G_{a} + G + g) + S(S + \omega C_{ga})}{(G_{a} + G)^{2} + (S + \omega C_{ga})^{2}} \omega C_{ga}$$

The magnitude of *m* is

$$m = \left\{ \frac{(\omega C_{ga})^2 + g^2}{(G_a + G)^2 + (S + \omega C_{ga})^2} \right\}^{\frac{1}{2}} \dots (5)$$

 $\approx \frac{g(\mathbf{I} + \omega C_{ga}/2g)}{\{(G_a + G)^2 + (S + \omega C_{ga})^2\}^{\frac{1}{2}}} \quad (6)$

assuming $\omega C_{ya} < < g$.

4. The Anode Circuit Load

As an example of a load circuit which fulfils very approximately the conditions already specified in section I, we may assume a coil of inductance L and resistance R, tuned by a parallel connected condenser of capacity C. The admittance of such a circuit is given by

$$\dot{y} = \frac{R}{R^2 + \omega^2 L^2} + j \left(\omega C - \frac{\omega L}{R^2 + \omega^2 L^2} \right) \dots (7)$$

i.e., very approximately

$$\dot{y} = \frac{R}{\omega^2 L^2} + j \left(\omega C - \frac{I}{\omega L} \right) \dots \dots (8)$$

if $R^2 < \leq \omega^2 L^2$. This will be abbreviated to $\dot{v} = G + iS$... (9)

For variation of C, the admittance is that of a constant resistance (the so-called "dynamic" resistance of the tuned circuit) in parallel with a variable reactance. The same is very approximately true of variation with respect to frequency, since G will change comparatively little over the narrow range of frequency covered by the resonance curve.

The similar description of the tuned radiofrequency transformer and the audiofrequency transformer is quite familiar and need not be detailed.

In the following, therefore, it will be assumed, unless otherwise stated, that G is constant and S variable, either with frequency or circuit tuning.

5. The Circle Diagrams for Input Admittance and Voltage amplification

The complex quantity \dot{r} defined by

$$\dot{r} = (\dot{a} + \dot{b}\epsilon^{-j\theta})$$

where \dot{a} and \dot{b} are constant complex numbers (or vectors) and θ is a variable angle, describes a circle of radius b (the magnitude of \dot{b}) having its centre at \dot{a} . The maximum and minimum values of \dot{r} are clearly $(\dot{a} \pm b)\epsilon^{ja}$, a being the inclination of \dot{a} , and occur where $\dot{b}\epsilon^{j\theta}$ is parallel to and in opposition to \dot{a} respectively.

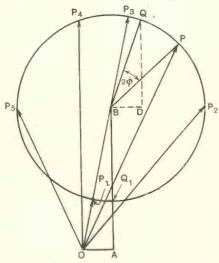
$$\dot{y}_{0} = \frac{\omega C_{ga}}{2(G_{a} + G)} \left[\{ \omega C_{ga} + j(g + 2G_{a} + G) \} + (\omega C_{ga} + jg)\epsilon^{-2j\phi} \right] .. (10)$$
$$\dot{m} = \frac{j\omega C_{ga} - g}{2(G_{a} + G)} (1 + \epsilon^{-2j\phi}) ... (11)$$

where

$$\tan \phi = \frac{S + \omega C_{ga}}{G_a + G} \qquad \dots \qquad (12)$$

These expressions look somewhat cumbersome, but the corresponding diagrams are quite simple in form. They are shown in Figs. 3 and 4. (The quantity ωC_{ga} is here considered as a constant. The circular form will be very approximately valid even when ω is the variable, provided, as is usually the case, the variation of ϕ (*i.e.*, of S) with frequency is very much more rapid than that of ω .)

It will be seen at once that the input admittance has a positive component (corresponding to a capacity) and a conductance component which may be negative over a considerable range of load variation.



 $\begin{array}{l} \operatorname{Fig. 3.} & -OA = BD = k \cdot \omega C_{ga}; \ AB = jk(g + 2G_a + G); \\ DQ = jk \cdot g; \ where \ k = \frac{\omega C_{ga}}{2(G_a + G)}; \ OB = k \cdot \{\omega C_{ga} + j \\ (g + 2G_a + 2G)\}; \ BQ = k\{\omega C_{ga} + jg\}; \ OP = \dot{y}_0. \end{array}$

The relative magnitudes involved in the above diagrams will, of course, depend on

December, 1933

particular cases. For illustration, the following valve quantities will be assumed.

$$G_a = \frac{I}{R_a} = \frac{I}{50,000} \text{ ohms}$$

= 20 × 10⁻⁶ ohms⁻¹
g = I m.a. per volt
= 1,000 × 10⁻⁶ ohms⁻¹

$$\mu = 50$$

 $C_{aa} = 4\mu\mu$ F

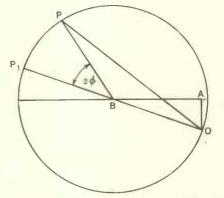


Fig. 4.—
$$OA = j\omega C_{ga}$$
; $AB = -g$; $OB = BP_1$
 $= j\omega C_{ga} - g$; $BP = (j\omega C_{ga} - g)\epsilon^{-2j\phi}$; $OP = \dot{m}$.

The constant value of G (the conductance component of the anode circuit admittance) will be taken as

$$G = \frac{I}{200,000}$$
 ohms = 5 × 10⁻⁶ ohms⁻¹

The forms taken by the diagrams for audioand radio₁frequencies will be considered separately.

6. The Circle Diagrams for Audio-Frequencies

At audio-frequencies ωC_{ga} will be negligible compared with g. Thus at 10 kc/s. ωC_{ga} will be only about 0.25×10^{-6} ohms⁻¹. The diagrams are then as shown in Figs. 5 and 6. The following particular points may be noted.

(a) G_0 is negative for all negative values of ϕ , *i.e.*, for all inductive loads. The maximum negative value of G_0 occurs when $2\phi = -\pi/2$, *i.e.*, G = -S, and is given by

$$G_0(\text{neg.max.}) = \frac{g}{2(G_a + G)} \,\omega C_{ga} \,\text{ohms}^{-1} \dots (I3)$$

This is 5×10^{-6} ohms⁻¹ (*i.e.*, a shunt resistance of 200,000) for the typical case quoted.

(b) The maximum positive value of G_0 is as in (a).

1.e.,

December, 1933

(c) The maximum value of y_0 is capacitive and occurs when $\phi = 0$ (*i.e.*, S = 0, the load being tuned or purely resistive). It is given by

$$y_0(\text{max.}) = S_0(\text{max.}) = \frac{(g+G_a+G)}{G_a+G} \omega C_{ga}$$
(14)

This is equivalent to $164\mu\mu$ F. for the numerical case.

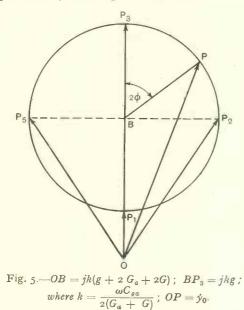
(d) The maximum value of m occurs when S = o (*i.e.*, when the circuit is tuned) and is given by

$$m = \frac{g}{G_a + G} \qquad \dots \qquad (15)$$

In an article on "Oscillation in Tuned Radio-frequency Amplifiers" (P.I.R.E., Vol. 19, pp. 421-437) B. J. Thompson gives a limiting stability formula for a tuned r.f. stage using a screen-grid valve, derived from considerations of energy. His formula is immediately derivable from eq. 13 of sect. 6. Thompson gives very satisfactory experimental confirmation of the formula.

7. A Screen-grid Valve at Radio-Frequencies

As already pointed out in section I, the quantities μ and G_a are far from constant



in a screen-grid valve, and will vary appreciably with conditions of operation. Within these limitations, however, the smallness of C_{ga} in the screen-grid value, and the consequent smallness of ωC_{ga} even at radiofrequencies, makes this case comparable with that of the ordinary triode at audio-

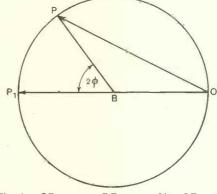


Fig. 6.—OB = -g; $BP = -g^{-2j\phi}$; $OP = \dot{m}$.

frequencies. The conclusions of section 6 can, therefore, be taken as, at least, an indication of the nature of the variation of the input admittance and amplification of the screen-grid valve.

8. Triode Valve at Radio-Frequencies

At a frequency of 10^6 cycles per second, ωC_{aa} for the example given in section 5 will be 25×10^{-6} . This is comparable with G_a . The circle diagrams will therefore be as in Figs. 3 and 4, except that in these diagrams OA and AQ_1 are somewhat exaggerated relative to AB for the sake of clearness. The following particular points may be noted for comparison with corresponding conclusions of section 6.

(a) G_0 is not negative for all values of inductive anode load, but only for those for which P lies to the left of O. The maximum positive and negative values of G_0 are given by

$$G_0 (\text{max.}) = \frac{\omega C_{ga}}{2(G_a + G)} \left\{ \sqrt{\omega^2 C_{ga}^2 + g^2} \pm \omega C_{ga} \right\}$$

For the numerical example

 G_0 (max.) = + 525 × 10⁻⁶; - 475 × 10⁻⁶.

Thus the negative input shunt resistance reaches in this case the very low figure of about 2,000 ohms. It is, of course, this low negative input resistance which accounts for the instability of un-neutrodyned tunedcircuit triode-valve amplifying stages.

EXPERIMENTAL WIRELESS

(b) The maximum value of m is

$$m \text{ (max.)} = \frac{\sqrt{g^2 + \omega C_{ga}^2}}{G_a + G} \qquad \dots \qquad (17)$$

and occurs when $\phi = 0$, *i.e.*,

(*i.e.*, the circuit is tuned by its own capacity plus the grid-anode and anode-filament capacities). For the numerical example

$$m (max.) = 40.$$

(c) The input admittance at maximum amplification is given by

$$\dot{y}_{0} = \frac{(\omega C_{ga})^{2}}{G_{a} + G} + j \frac{g + G_{a} + G}{G_{a} + G} \omega C_{ga} \qquad (19)$$
$$= 25 \times 10^{-6} + j 1025 \times 10^{-6}$$

i.e., a resistance of 40,000 ohms in parallel with a capacity of 164 $\mu\mu$ F.

(d) The maximum value of y_0 is not that associated with maximum amplification, but the difference is very little in practice (c.f., OP_3 and OQ in Fig. 4).

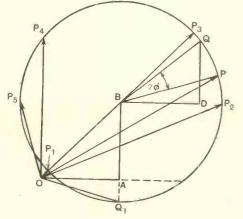


Fig. 7.— $OA = BD = k \cdot \omega C_{ga}$; $AB = j \cdot k(g + 2)$ $G_a + 2G$; $DQ = j \cdot k \cdot g$; where $k = \frac{\omega C_{ga}}{2(G_a + G)}$; $OB = k\{\omega C_{ga} + j(g + 2)G_a + 2G\}$; BQ = k $\{\omega C_{ga} + jg\}$; $OP = f_0$.

Of the above, the most important points are the low value of negative input resistance for an inductive load, and the fact that at the maximum amplification setting the input conductance is positive and not very large, the input admittance being practically capacitive.

9. Input Admittance and Amplification at Very High Radio-Frequencies

At very high frequencies (e.g., 10^7 c/s.) ωC_{ga} becomes correspondingly large (250 \times 10⁻⁶ for the case considered in (6)). The input admittance diagram will then become as in Fig. 7. The conclusions of section 8 are not thereby modified, but it is interesting to note that there is a possibility of a range of negative (*i.e.*, inductive) values for the input admittance for large values of 2ϕ (i.e., for large values of the susceptance components of the anode circuit admittance). The point is, however, mainly of theoretical interest. Of more practical interest are the very low values reached by G_0 at the maximum positive and negative conditions. For the typical numerical example these values correspond to input shunt resistances of about + 150 and - 250 ohms respectively.

10. Summary

In a triode valve amplifying stage of which the external anode circuit admittance, including the anode-filament capacity, can be represented as a constant conductance G in parallel with a variable susceptance S, the variation of the principal part of the input admittance, *i.e.*, that part which is due to coupling through the grid-anode capacity, can be represented by means of a simple circle diagram. The voltage amplification given by the stage can be similarly represented.

The principal formulæ derived are restated here for convenience of reference and comparison.

Load admittance = G + jS.

Valve conductance, G_a ; mutual conductance g; grid-anode capacity C_{ga} .

Input admittance = $G_0 + jS_0$.

(a) The maximum positive and negative values of G_0 occur when $G = \pm S$ approximately, and are given by

$$G_0 = \frac{\omega C_{ga}}{2(G_a + G)} \left\{ \sqrt{\omega^2 C_{ga}^2 + g^2} \pm \omega C_{ga} \right\}$$

In most practical cases, this is very approximately

$$G_0 = \frac{g}{G_a + G} \frac{\omega C_{ga}}{2}$$

(b) The maximum amplification occurs when $S = -\omega C_{gg}$.

December, 1933

Putting M for this maximum value,

$$M = \frac{\sqrt{g^2 + \omega^2 C_{ga}^2}}{G_a + G}$$
$$= \frac{g}{G_a + G} \text{ very approximately.}$$

(c) At maximum amplification

$$G_0 = \frac{(\omega C_{ga})^2}{G_a + G} = \frac{M}{g} (\omega C_{ga})^2$$
$$S_0 = \frac{(g + G_a + G)}{(G_a + G)} \omega C_{ga} = (M + I) \omega C_{ga}$$

(d) For any values G and S (anode circuit conductance and susceptance)

$$G_{0} = \frac{\omega C_{ga}(G_{a} + G + g) + gS}{(G_{a} + G)^{2} + (S + \omega C_{ga})^{2}} \omega C_{ga}$$

$$S_{0} = \frac{(G_{a} + G)(G_{a} + G + g) + S(S + \omega C_{ga})}{(G_{a} + G)^{2} + (S + \omega C_{ga})^{2}} \omega C_{ga}$$

and

$$m = \left\{ \frac{(\omega C_{ga})^2 + g^2}{(G_a + G)^2 + (S + \omega C_{ga})^2} \right\}^{\frac{1}{2}}$$

APPENDIX

Derivation of circle diagrams for \dot{y}_0 and \dot{m} .

$$\dot{y}_{0} = j\omega C_{ga} \frac{(g + G_{a} + G) + jS}{(G_{a} + G) + j(S + \omega C_{ga})}$$

$$= j\omega C_{ga} \left\{ \mathbf{I} + \frac{g - j\omega C_{ga}}{(G_{a} + G) + j(S + \omega C_{ga})} \right\}$$

$$= j\omega C_{ga} \left[\mathbf{I} + \frac{g - j\omega C_{ga}}{2(G_{a} + G)} \left\{ \mathbf{I} + \frac{(G_{a} + G) - j(S + \omega C_{ga})}{(G_{a} + G) + j(S + \omega C_{ga})} \right\} \right]$$

$$= j\omega C_{ga} \left[\mathbf{I} + \frac{g - j\omega C_{ga}}{2(G_{a} + G)} (\mathbf{I} + \epsilon^{-2j\phi}) \right]$$

where $\tan \phi = \frac{S + \omega C_{ga}}{G_a + G}$

$$= \frac{\omega C_{ga}}{2(G_a + G)} [\{\omega C_{ga} + j(g + 2G_a + 2G)\} + (\omega C_{ga} + jg)\epsilon^{-2j\phi}]$$

The derivation for *m* is similar.

Naval Wireless

I.E.E. Wireless Section, Chairman's Address

THE opening meeting of the I.E.E. Wireless Section was held on 1st November, when Mr. G. Shearing, O.B.E., B.Sc., M.I.E.E., delivered his inaugural address as Chairman of the Section.

In introducing his subject, the speaker referred to the ramifications of modern wireless and to the connections with physics and engineering practice in modern wireless work.

He then proceeded to give a broad account of naval wireless practice, beginning with a map of naval wireless stations throughout the world. The traffic concerned was long-distance point-topoint work from these stations to England, as well as traffic between ship and shore, and traffic between ships of a squadron, etc. The long-distance point-to-point work was done mostly on short waves, but the medium wave region was still of considerable importance in ship working.

The lecturer then described the equipment of ships, giving general information as to the type of transmitters and receivers used. Communication was practically entirely by telegraphy, radiotelephony being only very slightly used. Reception was entirely by earphone so that no great attention had to be paid to a power output-stage at the receiver. This also had the merit of keeping down the number of stages and giving a low noiselevel. The standard types of naval receiver cover the range of 15 kc/s to 23 Mc/s. W/t offices on ship are usually below deck and at some distance from the aerials, and the lecturer discussed the cabling arrangements feeding the aerials into the apparatus. A slide was also displayed illustrating the number of aerials and the difficulties of wireless installations on H.M. ships.

The speaker also discussed shadow and screening effects due to ship structure and superstructures, giving a theoretical reasoning which was well confirmed in the case of the particular ship for which it was calculated. Interference between transmitters and receivers on the same ship was also discussed; this was usually helped by the frequency separations involved, but precautions had to be taken against spurious radio-frequency noises generated in machine-leads. Voltage supplies to transmitters were now mostly by hightension alternators at 500 c/s, and receivers were increasingly using indirectly heated cathode valves deriving l.t. and h.t. from alternators.

The lecturer next discussed direction finding practice, which had, in the Navy, several important applications in addition to that of navigation. Various types of ship d.f. installations were described, with a discussion of the field-distortions giving rise to quadrantal error. Methods (due to Mr. C. Horton, of H.M. Signal School) were also described for correcting these errors. An automatic direction-finder was also described and demonstrated in operation cn a local signal.

Dealing with recent advances in wireless generally, the speaker referred particularly to various new types and tendencies in valves. He then discussed some of the recent progress in working on wavelengths below to metres, describing several new methods of generating greater power at these ultra short waves. A new magnetron for about I metre working was demonstrated in operation. Finally, the lecturer dealt briefly with the changes of frequency-allocation arising out of the Madrid Conference and Lucerne plan.

Correspondence

Letters of technical interest are always welcome. In publishing such communications the Editors do not necessarily endorse any technical or general statements which they may contain.

Beat Frequency Oscillator

To the Editor, The Wireless Engineer.

SIR,—In your issue for September is an article by M. F. Cooper and L. G. Page, which describes an audio-oscillator, and contains an oscillogram of the ripple in the high tension supply.

Present with others is a component having a frequency of 3.3 to 3.4 kc. This, we are told, "is a record of the valve hiss." No possibility exists that it may be anything else; in spite of the fact that valve hiss, like the surface noise picked up from a gramophone record, is an aperiodic phenomenon, and the recorded wave shows a very definite form even on the half-tone illustration, those responsible for the statement jump thoughtlessly out of the frying pan of improbability into the all-consuming fire of assertion.

Even in the improbable event of the recording oscillograph resonating at so low a frequency, or of some suitably placed LC product being maintained in oscillation at its natural frequency by the valve hiss, the statement to which objection has been taken still cannot be justified, since the oscillogram would be in no wise a record of the valve hiss, but merely of its presence.

It would therefore clear matters up if the authors would put forward their grounds for making the statement. ARCHIBALD W. STEWART.

Whitefield, Manchester.

Applications of the Dynatron

To the Editor, The Wireless Engineer

SIR,—In his very interesting article on "Applications of the Dynatron," published in your issue dated October, 1933, Mr. Scroggie describes an application of the technique of automatic gain control to the dynatron circuit. He refers to a paper by Arguimbau (*P.I.R.E.*, Jan., 1933) as being, to his knowledge, the only paper describing a similar idea. It may therefore be of interest to him and to your readers to know that Dr. J. Groszkowski has already published a description of a dynatron oscillator with automatic grid-bias control, the circuit being essentially the same as that arrived at independently by Mr. Scroggie. Groszkowski's paper also contains experimental data illustrating the great improvement in frequency-stability with respect to operating conditions which is obtainable in this way. The paper is, unfortunately, in Polish (*Przeglad Radjotechniczny*, May 15th, 1933), but it is hoped to arrange for the publication of an English version in the near future.

I may say that after the publication of Arguimbau's paper, I carried the amplitude-control idea described in it a stage further, and constructed a self-maintained triode oscillator circuit in which very full control of the amplitude was obtained by means of an associated automatic-volume-control type of amplifier, having a controllable maximum output-voltage. With this arrangement it was possible to maintain oscillation over almost any desired range of the so-called "straight" part of the oscillator characteristic, however small. It is hoped to publish a brief description of this work at a later date.

In the course of his article, Mr. Scroggie referred to certain papers of my own on the characteristics and advantages of the dynatron circuit. While I am prepared to endorse practically everything Mr. Scroggie has said about the merits and practical usefulness of this very attractive circuit, I must confess that my earlier enthusiasm has been tempered somewhat by subsequent experience, at least as far as frequency stability is concerned. It is true that the frequency can be made very satisfactorily independent of small changes in the supply voltages, but in some cases I have encountered a small but persistent frequency drift which appeared to be due to a corresponding small but steady change in secondary emission (the agency responsible for the negative-resistance characteristic). The variability of the secondary-emission effects as between different valves of the same type, a point mentioned by Mr. Scroggie, suggests that secondary emission is critically dependent on the nature of the surface of the emitting electrode which surface may itself be affected by the intensity and duration of the secondary emission. It would be interesting to know if Mr. Scroggie has any data on the longperiod constancy of secondary emission in small receiving tetrodes. It is true that the direct effect on the frequency of any consequent variation of the negative slope of the characteristic may be expected to be very small, but there is a larger indirect effect on frequency arising from the de-pendence of interelectrode capacitance on the space-charge. (See Baker, J. I.E.E., August, 1933). F. M. Collebrook.

Teddington, Middlesex.

To the Editor, The Wireless Engineer

SIR,—I am obliged to Mr. Colebrook for drawing my attention to Groszkowski's paper on oscillation amplitude control. Unfortunately, the Polish language has been outside my education, and in any case the paper appeared some months after my own was submitted. Quite a number of valuable contributions, more especially on the frequency maintenance question, have appeared since; and some of these were included in my bibliography.

As the great bulk of the literature on the subject is either purely theoretical, or refers to extremely precise and specialised practice I felt that there was room for information of a more workaday character. My references to frequency stability, must therefore be interpreted on this understanding, and I would not presume to give an original opinion as to the possible degree of constancy. I understand, however, that Mr. Griffiths's recent paper on this subject is founded on extensive experience of the work in which Mr. Colebrook expresses interest.

My own less systematic work does nevertheless support Mr. Colebrook's statement that the secondary emission is critically dependent on the nature of the surface of the emitting electrode; which may be considerably changed, or even ruined, by over-running the valve : hence my advice to limit the screen current.

I am interested to learn that Mr. Colebrook has carried into effect the idea of amplified amplitude control. My attempts to obtain extreme constancy in this way failed, because the time constant of the bias control circuit, which had to be sufficiently great to prevent amplified oscillations from being fed back to the oscillator, led to intermittency of oscillation. In fact, stable control appeared to be possible only if the control rectifier damped the oscillatory circuit to a certain minimum extent ; which was one of the things the system was designed to avoid, with the object of minimising harmonics.

These tests were confined entirely to dynatron oscillators; which appeared the most hopeful by reason, among other things, of the high degree of control exercised by the grid bias voltage. I very much hope that Mr. Colebrook's work on triode oscillators will be published. I am also hopeful that those better qualified than

myself may be able to explain satisfactorily the apparent discrepancy between theory and practice, noted towards the end of my paper; as it is of some practical importance.

M. G. SCROGGIE.

Upper Norwood, S.E.19.

To the Editor, The Wireless Engineer

SIR,-In your October issue M. G. Scroggie described the single circuit S.G. precision radio oscillator. Passing on to my double circuit oscillator (radio and audio) patent 310915, he says: "the precision is lower." If an audio circuit is put in series with the radio circuit there is a slight frequency change. But if the double circuit oscillator is calibrated as such, the precision is alike in the two cases.

It may be of interest to remark that crystal control is treated in 310915 (claim 6), and I have used it experimentally. Fig. 11 of Mr. Scroggie's article is a modification of Fig. 4 (claim 9) of 310915 of which he was obviously unaware.

Referring to the use of valves having low anode to grid capacity for precision oscillators, the first valve of this kind was made to my specification by the Osram Co. in 1929. It was used by Messrs. H. W. Sullivan in their oscillator at the Physical H. W. Sullivan III then obtained society Exhibition in January, 1930. N. W. McLachlan.

Philips's Receiver—Dynamic Resistance

To the Editor, The Wireless Engineer

SIR,-I beg to refer to a statement regarding Philips's 634 Superinductance Receiver, appearing in the October issue of THE WIRELESS ENGINEER. The paragraph concerned reads as follows :--

"But in a number of receivers tuned circuits of high dynamic resistance are secured by operating the radio frequency amplifier with a controlled amount of regeneration. For example, Philips's 634A Superinductance Receiver, in addition to exceptionally good coils, has a potentiometer ganged to the tuning control which, by varying the bias of one of the H.F. valves, keeps the receiver just within the limits of stability throughout the waveband . . .

Your statement gives the impression that reac-tion is an essential feature of the design of the Philips's 634 receiver and that the high dynamic resistance of the tuned circuits in this set is obtained by deliberate and controlled regeneration. This is not the case. The exceptional efficiency of these circuits is obtained by careful electrical and mechanical design and by highly specialised methods of production, whereby the electrical losses in all components associated with the tuned circuits are reduced to an extremely low value.

The actual purpose of the coupled potentiometer is to produce even sensitivity over the waveband by reducing the excessive gain which would otherwise occur on the lower wave lengths with a circuit arrangement of this nature.

London, W.C.2.

A. B. CALKIN, Philips Lamps, Ltd.

Double Channel Transmission

To the Editor, The Wireless Engineer

SIR,-I hope you may see your way in the near future to give space for discussion on an old subject which seems to be receiving more attention of late. There are several points obscure to me which if ever I venture to mention are usually "side tracked." Are engineers afraid to tackle them? acked." Are engineers afraid to tackle them? What is "stereoscopic" effect? Is it not in

itself an illusion, if so would not any other successful illusion answer as well or better? The stock explanation is the "one eye—two eye" analogy. Am I abnormal when I claim to be able to see perfectly well with one eye and that the only difficulty is of focusing; one eye alone is capable of appreciating "depth." I suggest there are infinitely more than "double channel" lines of vision which enable us to appreciate perspective. Just the same with the ear for which member the focusing difficulty only is more apparent. Music seems no less real to me heard with only one ear. We do have reason to believe that each frequency is conveyed separately to the brain while is it not dangerous to assume, as is done, that we are so tolerant of phase displacement in reproduction ?

I humbly suggest that radio engineers might aim higher than the "double channel" idea and concentrate on what constitutes perfect reproduction of sound not forgetting at the same time that certain illusion might be permissible as a means to an end.

Quite obviously the microphone has similar defects to a photographic plate but why assume that two microphones or two transmission lines to two ears are likely to be a good solution to the problem ?

The need seems to be to contrive a "microphone "which is in itself a perfect "ear " and works on similar principles to the human organ, to " scan " if necessary the audio frequencies and render them separately as far as is possible at the producing end. Failing all this at least to try the effect of faithful phasing.

Ware.

GERALD SAYERS.

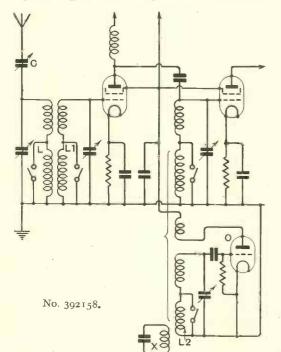
Some Recent Patents

The following abstracts are prepared, with the permission of the Controller of H.M. Stationery Office, from Specifications obtainable at the Patent Office, 25, Southampton Buildings, London, W.C.2, price 1/- each.

SUPERHET RECEIVERS

Application date, 9th November, 1931. No. 392158

In order to preserve a constant ratio between the tuned input and local oscillator circuits in a superhet set, so as to permit single-knob tuning over both the medium and long wave-bands, a "compound" impedance (preferably a loop circuit of inductance



and capacity) is coupled to the long-wave or loading inductance of one of the circuits. As shown, the aerial is connected through a condenser C to a band-pass input comprising switch-operated loadingcoils L, L_1 , the auxiliary "compound" impedance X being coupled to the loading-coil L_2 in the grid circuit of the local oscillator valve O.

Patent issued to The Plessey Co., Ltd., and C. E. G. Bailey.

PREVENTING MAINS "HUM."

Convention date (Germany), 23rd November, 1931 No. 393495

In certain types of mains-driven valve, the filament and cathode are separated by a discharge space which carries a minor or auxiliary electron stream. Since the latter fluctuates with the potential and temperature of the filament, it tends to set up "hum." According to the invention this is prevented by tapping-off, from a resistance inserted between the anode and cathode, a biasing potential sufficient to saturate the discharge-space in question. A different tapping from the same resistance supplies the biasing-voltage for the control grid. Patent issued to Telefunken Ges für drahtlose Telegraphie m.b.h.

H.F. AMPLIFIERS

Convention date (Germany), 29th February, 1932 No. 393553

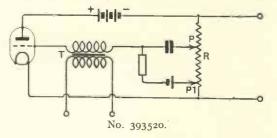
When using screen-grid valves for amplifying ultra high frequencies it is desirable, in order to avoid undesirable reaction effects, to maintain the screen-grid as nearly as possible at the same high-frequency potential, *i.e.*, for the working frequency. In order to achieve this result the screen grid is connected to the cathode through two condensers in series, and the anode is connected to the cathode through a third condenser. The inherent capacity between the screen-grid and anode inside then forms the fourth side of a balanced bridge, and the output impedance is connected across a diagonal.

Patent issued to Telefunken Ges fur drahtlose Telegraphie m.b.h.

AMPLIFIER CIRCUITS

Convention date (Germany), 29th December, 1931 No. 393520

Distortion due to curvature in the valve-characteristic, or to some undesired variation of the external circuit impedance, is compensated by feedingback to the grid from a tapping P on the resistance R an AC component in phase-opposition with the AC component to be corrected. Another tapping P_{I} supplies grid-bias voltage through the output transformer T. In a modified arrangement



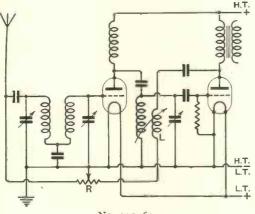
the two tappings are taken from different parallel resistances, both shunting the anode-cathode circuit.

Patent issued to Telefunken Ges für drahtlose Telegraphie.

VOLUME CONTROL

Application date, 23rd September, 1931. No. 391469

Part of the volume-control potentiometer R is arranged in shunt with the aerial circuit, whilst the remainder is in series with the reaction coil L. As the earthed tapping-point is moved to the left to reduce volume, the series resistance in the re-



No. 391469.

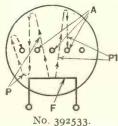
action is increased, thereby preventing overloading. Patent issued to The Paragon Rubber Mftg. Co., Ltd.

SHORT-WAVE GENERATORS

Convention date (U.S.A.), 4th December, 1930. No. 392533

As shown in the Figure the electron emitter Fco-operates with a second electrode A, which may be a perforated plate or any similar grid-like structure, provided the total area of the spaces

parts.



oscillations are determined by the potential applied across the "grid" A and filament F, and are due to the elongated path taken by the bulk of the electron stream, as indicated at Pand PI.

or perforations is large compared with the projected area of the solid The frequency and

amplitude of the generated

Patent issued to Marconi's Wireless Telegraph Co., Ltd.

SHORT-WAVE SYSTEMS

Application dates 5th November and 18th November, 1931, and 4th March, 1932. No. 392210

Relates to a system of generating and receiving ultra-short waves by the Barkhausen-Kurz method. The valves are operated in push-pull and are

coupled through tuned Lecher-wires to dipole aerials of various forms, some of which are designed to produce high-directive effects. Two or more pairs of valves may be coupled together by connecting the filament circuits through tuned Lecherwires. Various methods of applying the necessary operating potentials are described, together with a special "optical image" arrangement of the valve electrodes to ensure symmetry. Modulating signals may be applied either to the plate or grid, and the receiving circuits may be designed to give super-regenerative amplification. Patent issued to Marconi's Wireless Telegraph

Co., Ltd., and G. A. Mathieu.

TELEVISION RECEIVERS

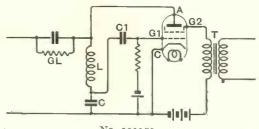
Convention date (U.S.A.), 15th January, 1932. No. 392869

The characteristic greenish appearance of the picture reproduced on the fluorescent screen of a cathode-ray television receiver is converted into a more natural and pleasing colour by projecting on to the screen, simultaneously with the received picture, a beam of unmodulated monochromatic light, preferably complementary to the fluorescent colour. The compensating light is derived from one or more auxiliary lamps mounted in close proximity to the receiving surface, but screened from direct observation. A similar method may be used to offset the characteristic colour effect due to Neon and similar lamps used in other types of television receivers.

Patent issued to Marconi's Wireless Telegraph Co., Ltd.

DETECTOR-AMPLIFIERS

Application date, 13th May, 1932. No. 391979 A screen-grid valve of normal type is used as a combined diode rectifier and L.F. amplifier. The



No. 391979.

modulated signal energy is applied across the anode A and cathode C through a grid leak combination GL. Rectified currents are fed from the junction of a coil L and condenser C (forming a radio-frequency shunt) through a condenser CI to the control grid GI, the usual screen-grid G2 being coupled to the next stage through a low-frequency transformer T. If a pentode valve is connected up in a similar manner, the extra electrode can be used as a spacecharge grid.

Patent issued to Marconi's Wireless Telegraph Co., Ltd.

INDEX

VOL. X. The Wireless Engineer & Experimental Wireless 1933

I. GENERAL INDEX

PAGE A bac for Single-layer Coils, H. Seki .. I2 Abacs for Measuring Resistances 553, 554 ABSTRACTS AND REFERENCES (see separate Index) (Correspondence) . . 492 Acoustical Performance of a Cone-type Loud Amplification of Transients, C. H. Smith 206 Amplifier Circuits (Patents)234, 290, 665Amplifiers, Gas-filled (Patents)583 347, 665 • • 523 . . Amplifiers, Screen-grid (Patents) 583 Amplifiers, Tone Correcting, G. Priechenfried 487 Amplitude of Loud Speaker Diaphragms at Low Frequencies, N. W. McLachlan 375 Application of the Dynatron, M. G. Scroggie.. 527 (Correspondence) ... 663 Attenuation of Transmission Lines, M. J. O. 139 120 Automatic Tone Compensation (Patents) 233 . . 349, 524, 642 Automatic Volume Control for Radio Re-248 ceivers, C. B. Fisher . . Balancing and Stabilising of H.F. Ampli-fiers (I.E.E. paper), W. Ure, E. J. Grainger, and H. R. Cantelo 259 Band-pass Filters (*Patents*) Band-pass Tuners (*Patents*) Beam Systems (*Patents*) Beat Frequency Oscillator, M. F. Cooper and 348 522 407 469 663 BOOKS RECEIVED 25, 88, 196, 374 BOOK REVIEWS : Alternating Current Electrical Engineering, P. Kemp 433 Atmospheric Electricity, B. F. J. Schonland 137 Einführung in die Schwingungslehre, Dr. 138 Barkhausen. Electron Tubes and their Application, J. H. Morecroft 556

Elements of Engineering Acoustics. L.E.C.	
Hughes	656
Principles of Electromagnetism, E. B.	
Moullin	61
Radio Engineering, F. E. Terman	316
Short-wave Wireless Communication, A. W.	
Ladner and C. R. Stoner	138
Theory of Thermionic Vacuum Tubes, E. L.	
Chaffee	380

	PAGE
Broadcast Relay Systems (Patents)	466
Broadcasting on 7.85 Metres in Amsterdam,	4
P. J. H. A. Nordlohne	186
Bush Radio, Baird Television Receiver (Illus-	100
	= +0
tration)	540
Cabinet Sets (Patents)	641
Capacitive or Capacitative (Editorial)	I
(Correspondence)	145
Cath Janes J. J. Ameril: Game (Defaute)	289
Cathode-coupled Ampliners (Patents).	209
Cathode-ray Oscillograph at Ultra-high Frequencies, Use of, H. E. Hollmann 430	0
Frequencies, Use of, H. E. Holimann 430	, 484
Cathode Ray Oscillograph in Radio Research	
(Editorial)	251
	, 466
Cathode-ray Tube, New High-Efficiency, M.	
von Ardenne	502
von Ardenne Cathode-ray Tubes (<i>Patents</i>) 350, 466 Cathodes, High-emission (<i>Patents</i>)	644
Cathodes High-emission (Patents)	280
Cathin Value Orresp and Marsoni	209
Catkin Valve, Osram and Marconi	295
Change of Address	254
Characteristics of Short-wave Propagation	
(<i>I.E.E. Paper</i>), Prof. J. Hollingworth Circle Diagrams of Valve Input Admittance	89
Circle Diagrams of Valve Input Admittance	
and Amplification Factor. F. M. Cole-	
brook	657
Circularly-polarised Radiation (Patents)	176
Civil Aviation Signal Services, Choice of	-/0
Wavelengths, N. F. S. Hecht and H. L.	
	506
Crowther	596
Coils, Iron Powder Compound Cores for	
(Editorial)	I
Coils, Iron Core Tuning (Editorial)	293
Cold-cathode Valves (Patents)	345
Cole, E. K. Ltd., Capacity-Matching Bridge	
(Tllaucturations)	76
	, 643
Combined Transmitter and Receivers (Patents)	582
Constant-Coupling Systems (Patents) . 408	644
Constant-frequency Generators (Patents)	350
	642
Constant-sensitivity Couplings (Patents)	641
Cooling H.F. Apparatus (Patents)	56
CORRESPONDENCE, 26, 145, 202, 257, 313, 369	
491, 555, 612	, 663
Coupling Circuits (Patents)	642
Decoupling Efficiency, W. A. Barclay	307
(Convertion damen)	
Decrement of Tuned Circuits, Optimum, D. A.	612
Bell	371
Demodulation under Practical Conditions,	
M. V. Callendar	480
(Correspondence)	612
Detector-Amplifiers (Patents)	666
Detector ()scillators (Patents)	235
Detectors or Rectifiers (Patents)	23
Diaphragm, Paper Cone, Coil-driven, Vibra-	-3.
a superior outer outer vitter vitte	

tions of, F. R. W. Strafford 141

	AGE
Diode as a Cumulative Grid Rectifier, E. A.	
Biedermann	123
Direction-Finding (Patents) 120, 584.	586
Biedermann Direction-Finding (<i>Patents</i>) . 120, 584, Distortion Cancellation in Audio Amplifiers,	5.
W. Baggally	413
Double Channel Transmission (Correspondence)	664
Dry Contact Bectifiers (Patents) 57 177 406	- 84
Dry-Contact Rectifiers (<i>Patents</i>) 57, 177, 466, Dynatron, Application of, M. G. Scroggie	504
Dynation, Application of, M. G. Scröggle	527
(Correspondence)	663
(Correspondence). Dynatron Circuit, High Selectivity Voltage Amplification, F. M. Colebrook	
Amplification, F. M. Colebrook	69
(Correspondence)	204
Thisse Swan are weth Amplifor (Tiles	
Electrolytic Condensers (Patents)	-
tration)	144
Electrolytic Condensers (Patents)	524
Electromagnetic Induction (Editorial)	409
Electormagnetism, Principles of (Editorial) 61,	179
(Correspondence). 146, 202, 315, 429,	555
Electronic Oscillations and the Magnetron	000
Electronic Oscillations and the Magnetron Short-wave Oscillator (I.E.E. Paper)	
E C S Mercur	T 42
E. C. S. Megaw	142
Electrostatic Loud Speakers (Patents)	520
Errors in D.F. Calibrations of Steel Ships	
(I.E.E. Paper), J. F. Coates	434
EXHIBITIONS :	
Olympia Radio Show, 1933 (Illustration)	483
Olympia Radio Show, 1933, Review of Ex-	1 0
hibits	543
hibits	343
Physical Society 02	, 74
Ferrocast H.F. Coils, A. Schneider	183
Field Strength, Recording (B.B.C.	
Automatic Equipment), C. H. Smith	I 4
Automatic Equipment), C. H. Smith	14
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>)	14 520
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>)	
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>)	520
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>).	520 [.]
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>)	520 77
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>)	520 77
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>) Gramophone Amplifiers (<i>Patents</i>) Gramophone Pick-ups (<i>Patents</i>) 175, 349, 465,	520 77
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>) Gramophone Amplifiers (<i>Patents</i>) Gramophone Pick-ups (<i>Patents</i>) 175, 349, 465,	520 77
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli-	520 77 119 348 521
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>) Gramophone Amplifiers (<i>Patents</i>) Gramophone Pick-ups (<i>Patents</i>) 175, 349, 465,	520 77
Automatic Equipment), C. H. Smith Film Television (<i>Patents</i>) General Radio Apparatus for Measuring Receiver Characteristics (<i>Illustration</i>) "Glow-discharge" Amplifiers (<i>Patents</i>) Gramophone Amplifiers (<i>Patents</i>) Gramophone Pick-ups (<i>Patents</i>) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 77 119 348 521
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) H.F. Feeder Lines (Patents) H.F. Generators (Patents) H.F. Generators (Patents) H.F. Systems (Patents) High Power Pentode as an Electron-Coupled	520 ⁻ 77 119 348 521 65
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) H.F. Generators (Patents) H.F. Generators (Patents) H.F. Generators (Patents) H.F. Systems (Patents) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A.	520 77 119 348 521 65 147 292 290 555 407
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) H.F. Generators (Patents) H.F. Generators (Patents) H.F. Generators (Correspondence) H.F. Systems (Patents) High Power Pentode as an Electron-Coupled	520 77 119 348 521 65 147 292 290 555 407
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo	520 77 119 348 521 65 147 292 290 555 407
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo	520 77 119 348 521 65 147 292 290 555 407 648
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo	520 77 119 348 521 65 147 292 290 555 407
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Generators (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications,	520 77 119 348 521 65 147 292 290 555 5407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Generators (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications,	520 77 119 348 521 65 147 292 290 555 407 648
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) H.F. Feeder Lines (Patents) H.F. Generators (Patents) H.F. Generators (Patents) H.F. Systems (Patents) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr INSTITUTION OF ELECTRICAL ENGINEERS,	520 77 119 348 521 65 147 292 290 555 5407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) H.F. Systems (Patents) 177, 233, H.F. Systems (Patents) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr INSTITUTION OF ELECTRICAL ENGINEERS, PAPERS READ :	520 77 119 348 521 65 147 292 290 555 5407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) H.F. Systems (Patents) 177, 233, H.F. Systems (Patents) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr INSTITUTION OF ELECTRICAL ENGINEERS, PAPERS READ :	520 77 119 348 521 65 147 292 290 555 5407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr INSTITUTION OF ELECTRICAL ENGINEERS, PAPERS READ: Balancing and Stabilising of H.F. Ampli-	520 77 119 348 521 65 147 292 290 555 555 407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measuring Set, Modifications, A. T. Starr Instruction of Electrical Engineers, PAPERS READ : Balancing and Stabilising of H.F. Ampli- fiers, W. Ure, E. J. Grainger, and H. R. Cantel	520 77 119 348 521 65 147 292 290 555 555 407 648 146 609
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measuring Set, Modifications, A. T. Starr Instruction of Electrical Engineers, PAPERS READ : Balancing and Stabilising of H.F. Ampli- fiers, W. Ure, E. J. Grainger, and H. R. Cantel	520 77 119 348 521 65 147 292 290 555 555 407 648 146
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr Institution of Electrical Engineers, PAPERS READ : Balancing and Stabilising of H.F. Ampli- fiers, W. Ure, E. J. Grainger, and H. R. Cantel Characteristics of Short-wave Propagation,	520 77 119 348 521 65 147 292 290 555 407 648 146 609
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) H.F. Systems (Patents) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr INSTITUTION OF ELECTRICAL ENGINEERS, PAPERS READ: Balancing and Stabilising of H.F. Ampli- fiers, W. Ure, E. J. Grainger, and H. R. Cantel Characteristics of Short-wave Propagation, Prof. I. Hollingworth	520 77 119 348 521 65 147 292 290 555 555 407 648 146 609
Automatic Equipment), C. H. Smith Film Television (Patents) General Radio Apparatus for Measuring Receiver Characteristics (Illustration) "Glow-discharge" Amplifiers (Patents) Gramophone Amplifiers (Patents) Gramophone Pick-ups (Patents) 175, 349, 465, Grid Current Compensation in Power Ampli- fiers, W. Baggally Harmonic Content in Amplifiers (Corre- spondence) 26, H.F. Feeder Lines (Patents) 176, 178, H.F. Generators (Patents) 177, 233, H.F. Generators (Correspondence) High Power Pentode as an Electron-Coupled Transmitter, J. C. W. Drabble and R. A. Yeo Impedance Measurements (Correspondence) Impedance Measuring Set, Modifications, A. T. Starr Institution of Electrical Engineers, PAPERS READ : Balancing and Stabilising of H.F. Ampli- fiers, W. Ure, E. J. Grainger, and H. R. Cantel Characteristics of Short-wave Propagation,	520 77 119 348 521 65 147 292 290 555 407 648 146 609

	AGE
Errors in D.F. Calibrations of Steel Ships,	AGE
	12.4
	434 662
Operation of Several Broadcasting Stations	002
on the Same Wavelength, P. P. Eckersley	
	196
Radio Compass Developed in H.M. Signal	190
	434
Thermionic Valve, L. B. Turner	27
World Physics in Relation to Wireless,	•
Sir F. Smith (Kelvin Lecture) Interference Elimination (Patents), 176, 234, 3	317
Interference Elimination (Patents), 176, 234, 3	347,
348,	466
Interference with Broadcast Reception (Edi-	
torial) 237,	
Iron-content Cores for H.F. Coils, A.Schneider	183
(Correspondence)	313
	293
	4 91
Iron Powder Compound Cores for Coils	
(Editorial)	I
Iron-Powder Cores (Editorial)	467
Kemp, G. S., Obituary Notice	90
17	

Laminated or Non-laminated H.F. Core (Correspondence)	s?	
L (Correspondence)		49I
	н. н.	289
Light Intensifier (Patents)		119
Light-Sensitive Relays (Patents)		642
Loud Speaker, Cone-type, Acoustical P	er-	
formance of, D. A. Oliver		420
Loud-speaker Connections (Patents)		346
Loud Speaker Diaphragms, Amplitude of,	at	
Low Frequencies, N. W. McLachlan	• •	375
Loud-speaker Diaphragm (Patents)	• •	349
Loud Speakers (Patents), 60, 118, 176, 290,		
464, 520, 523,	524,	
Lucerne Wavelength Plan	• •	647
Magneto-Ionic Theory, J. A. Ratcliffe	• •	354
Magnetron Oscillator for Ultra-Short Wa	ve-	

TAT		
Magnetron Oscillator for Ultra-Short Wave	e-	
lengths, E. C. S. Megaw	•	197
	•	407
Mains Hum, Preventing (Patents)		665
Mains-Supply Units (Patents)		176
Man-made Static, P.O. Display at Olympia .		486
Marconi Company's Display at Physica	al	
Society's Exhibition (Illustration)		68
Measurement of Radio-frequency, Simplifica	a	
tion of, W. H. F. Griffiths 2	39,	299
(Correspondence)		369
Measuring Attenuation of Transmission Line	s,	
		139
Measuring Percentage Modulation (Patents) .		644
Measuring Resistances, W. A. Barclay .		552
Measuring the Self-capacitance of Coils, M. (3.	
Scroggie		477
Microphones, Ribbon (Patents)		408
"Midget" Receivers (Patents)		292
Mirror-drums for Television (Patents)		522
Modifications in the New Impedance Measu	r-	
ing Set. A. T. Starr		609
Modulating Systems (Patents)	45.	643

	PAGE
Monodial A.C. Super, Booklet.	90
Monodial A.C. Super, Booklet	
Fork for Frequency Control (Illustration)	75
Muirhead & Co.'s Precision Variable Con-	
	75
denser (Illustration) Multiplex Signalling (Patents)	0, 641
Multiplex Signalling (<i>Patents</i>)	
Scroggie	606
Scroggie Multi-range Mains-operated Valve Volt-	
meter, C. N. Smyth	I34
Multi-stage Amplifiers (Patents)	521
	5
auen Station (Editorial)	121
\blacksquare Naval Direction Finding (I.E.E.	
Naval Direction Finding (I.E.E. Papers), J. F. Coates and C. E. Horton	
and L. L.rampton	434
Naval Wireless (<i>I.E.E. Paper</i>), G. Shearing	662
New Abac for Single Layer Coils, H. Seki	12
New High-efficiency Cathode-ray Tube,	
	592
M. von Ardenne New Types of Broadcast Transmitting Aerials	
(Editorial)	525
Non-linear Valve Characteristics, C. S. Bull	.83
N.P.L. Annual Visit	412
N.P.L. New Radio Department	306
New York Contraction of the second seco	5
Ohmmeter, Multi-range Direct-reading, M.	
G. Scroggie	606
Olympia 1933, Review of Exhibits	543
(Correspondence)	664
Oscillator, Beat-Frequency, M. F. Cooper and L. G. Page	
L. G. Page	469
USCILLATOTS H. F. (Patents)	407
Optimum Decrement of Tuned Circuits for	
the Reception of Telephony, D. A. Bell	371
Output Stages, Choice of Valves for L.F.	07
Amplifiers, C. C. Whitehead	78
Descritic Oscillations Eliminating (Detute)	
Parasitic Oscillations, Eliminating (Patents)	521
Patent "Pool" in U.S.A.	18
PATENTS, 56, 118, 175, 233, 289, 345, 406, 464	, 520,
Pentagrid Converter, C. L. Lyons	
Pentada as an Electron coupled Transmitter	364
Pentode as an Electron-coupled Transmitter, J. C. W. Drabble and R. A. Yeo	6.8
Dentede Meduletere (Datente)	648
Pentode Modulators (Patents)	584
Philips' Receiver-Dynamic Resistance (Cor-	66.
respondence)	664
	7, 586
Physical Society's Exhibition	74
Picture-transmission Systems (Patents)	465
Piezo-Electric Couplings (Patents)	176
Piezo-Electric Oscillators (<i>Patents</i>) ,	292
Portable or Field Sets (Patents)	522
Pot Screens (Patents)	349
Powdered Magnetic Cores (Patents)	643
Pre-Set Condensers (Patents)	521
Principles of Electromagnetism (Editorial), 61	
(Correspondence). 146, 202, 315, 429	, 555
Fublication of Afficies	595
Push-Pull Circuits (Patents)	233

Juartz Vibr	ations, The	Researches	of the	е
late I				
E. H. Ray	yner			205

(

	PAGE
Radio Beacons (<i>Patents</i>)	59
Radio Compass Developed in H.M. Signal School (I.E.E. Paper), C. E.	
Signal School (I.E.E. Paper), C. F.	
Horton and C. Crampton	434
Horton and C. Crampton Reaction Control (<i>Patents</i>) 5 Receivers (<i>Patents</i>) 118, 291, 29 Receiver Circuit for Electrostatic Speaker	7, 408
Receivers (Patents) 118, 291, 29	2, 347
Receiver Circuit for Electrostatic Speaker	r -
(Patents)	584
(Patents)	289
Recording Field Strength, C. H. Smith	14
Rectifying Valves (<i>Patents</i>) 23 Remote Control (<i>Patents</i>)	3, 522
Remote Control (Patents) 34	6, 408
Researches of the late Dr. D. W. Dye on the	2
Vibrations of Quartz (I.E.E. Paper)	
	205
	552
reosistances, moasaring, w. m. barolog	
Schäffer, W. (Obituary Notice) Screened Grid Amplifiers (<i>Patents</i>), 59, 23 Selectivity Devices (<i>Patents</i>).	
canning Discs (Patents)	5, 340
Schaffer, W. (Obituary Notice)	258
Screened Grid Ampliners (Patents), 59, 230	0, 042
Selectivity Devices (Patents)	119
ing, M. G. Scroggie	477
Self-Tuned Amplifiers (<i>Patents</i>). S.G. Valve as a Superhet Detector, C. B Fisher	. 60
S.G. Valve as a Superhet Detector, C. B	
Fisher	541
Short-wave Aerials (Patents)	6, 585
Short-Wave Generators (Patents) 58, 58	5, 666
Short-Wave Propagation, Some Character	-
Fisher Short-wave Aerials (<i>Patents</i>) 58, 58 Short-Wave Generators (<i>Patents</i>) 58, 58 Short-Wave Propagation, Some Character istics (<i>I.E.E. Paper</i>), Prof. J. Holling- worth	-
worth	89 5, 583
Short-Wave Receivers (Patents)	5. 583
Short-Wave Systems (Patents)	666
Short-Wave Television (Patents)	280
Signalling Systems (Patents)	5, 464
Signalling to Aircraft (<i>Patents</i>) Simplification of Accurate Measurement of	f 50
Radio-frequency, W. H. F. Griffiths, 23	0 200
(Course boundarian)	260
(Correspondence) Sound Distribution from a Horn (Corre-	369
Sound Distribution from a from (Conte-	26
spondence)	8 -8-
Standard Audio-frequency Oscillator.	0, 505
Standard Audio-frequency Oscillator, /	303
Standard Telephone Co., Oscillator (Illus	ri 6
tration) Straight Sets v. Superheterodyne (Correspondence)	76
Straight Sets v. Superneterouyne (Corre-	
sponaence)	145
Sullivan-Griffiths Universal Wavemeter (Illus-	-
tration)	74
Sullivan Inductance Matching Set (Illus	
tration)	74
Superheterodyne Receivers (Patents), 59, 291	, 406,
584, 58	6,665
Super-Regenerative Circuits (Patents)	60
Super-Regenerative Circuits (<i>Patents</i>) Super-Regenerative Receivers (<i>Patents</i>) 29	0, 586
Television (Patents), 175, 235, 236, 289, 34.	5. 350.
464, 465, 520, 582, 64	4. 666
Television Receiver, Bush Radio, Baird Mirror-	-,
dram (Tillastration)	540
drum (Illustration) Theory and Practice of Tone Correction,	545
F. M. Colebrook	
10	5 270
(Correspondence) 31	5, 370
(Correspondence) 31 Thermionic Amplifiers (Patents) 177, 292, Thermionic Valve (I.E.E. Paper), L. B. Turner	400
Thermionic Valve (<i>I.E.E. Paper</i>), L. B. Turner	27

			- P	AUL
Tone Correcting Amplifiers, G.	Priech	enfried	1	487
Tone Correction, Theory and	Practi	ce, F.	M.	
Colebrook				4
(Correspondence)		20.14	315,	370
Transmitting Circuits (Patents)	. 4		236
Tuning Coils (Patents)	••		3 *	120
Tuning Controls (Patents)				59
Tuning Devices (Patents)				406
Tuning Dials (Patents)				583

Iltra-short Wave Broadcasting (7.85				
metres) in Amsterdam, P. J. H. A.				
Nordlohne	186			
Ultra-short-wave Generators (Patents)	522			
Ultra-short Wavelengths, A Magnetron	-			
Oscillator for, E. C. S. Megaw	197			
U.S.A. Patent "Pool"	18			
Use of Triode and Tetrode Valves for Measure-				
ment of D.C. Potential Differences, T. P.				
Hoar	19			
	-			
T T				
Valve Amplifiers (Patents) Valve Charactersitics, Non-linear, C. S.	347			
Valve Charactersitics, Non-linear, C. S.				
Bull	83			
Valve Construction, A New Idea (Catkin				
Valves)	295			
Valve Construction (Patents) 118,	345			
Valve Data Diagrams (Correspondence)	257			
Valve Input Admittance and Amplification				
Factor. Circle Diagrams, F. M. Colebrook	657			
Valve Voltmeter for Audio Frequencies	310			

Valve-Holders (Patents)	. 57			
Valve-Oscillators (Patents)	· 347			
TT I DT CI I ID I I I	. 290			
Valves (Patents) 350, 40	08, 644			
Valves, Pentode (Patents)				
Valves, Triode and Tetrode for Measurement				
of D.C. Potentials, T. P. Hoar	. 19			
Variable Condensers (Patents)				
Variable mu Valves (Patents)	75, 643			
Variable Resistances (Patents).				
Vibrations of a Coil-driven Paper Cone				
F. R. W. Strafford	57. 313			
Visual Tuning Indicators (Patents)	. 582			
Voltage Amplification with High Selectivit				
by means of the Dynatron Circuit, F. M	Í.			
COLEDIOUR	. 69			
Colebrook	. 69 1.			
Voltmeter Valve, Multi-range Mains-operated	1,			
Voltmeter Valve, Multi-range Mains-operated	1,			
Volume Control (<i>Patents</i>) 56, 177, 178, 40	1,			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (<i>Patents</i>) 56, 177, 178, 40	1, . 134 06, 666			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (<i>Patents</i>) 56, 177, 178, 40 XX /ave-band Adaptors (<i>Patents</i>)	1, 134 06, 666			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-Band Switching (Patents)	1, 134 06, 666 523 57			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (<i>Patents</i>) 56, 177, 178, 40 Wave-band Adaptors (<i>Patents</i>) Wave-Band Switching (<i>Patents</i>) Wave-change Switching (<i>Patents</i>)	1, 134 06,666 523 57 583			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (<i>Patents</i>) 56, 177, 178, 40 Wave-band Adaptors (<i>Patents</i>) Wave-Band Switching (<i>Patents</i>) Wave-change Switching (<i>Patents</i>) Wavemeter with Alternative Close and Operation	l, 134 06, 666 523 57 583 n			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (<i>Patents</i>) 56, 177, 178, 40 Wave-band Adaptors (<i>Patents</i>) Wave-Band Switching (<i>Patents</i>) Wave-change Switching (<i>Patents</i>) Wavemeter with Alternative Close and Operation	l, 134 06, 666 523 57 583 n			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-change Switching (Patents) Wave-change Switching (Patents) Wave-the and Switching (Patents) Wave-band Switching (Patents) Wave-change Switching (Patents) Wave-the and Switching (Patents) Wave-band Switching (Patents) Wave-band Switching (Patents) Wave-band Switching (Patents) Wave-band Switching (Patents)	1, 134 134 134 134 134 134 134 134			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-change Switching (Patents) Wave-change Switching (Patents) Wave-the change Switching (Patents) Wave-change Switching (Patents)	1, 1, 134 134 134 134 134 134 134 134			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-change Switching (Patents)	1, 134 06, 666 523 57 583 n 255 5- 309 119			
Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-change Switching (Patents) Wired-Wireless Systems (Patents), 235, 350, 5	1, 134 134 134 134 134 134 134 134			
 Voltmeter Valve, Multi-range Mains-operated C. N. Smyth Volume Control (Patents) 56, 177, 178, 40 Wave-band Adaptors (Patents) Wave-Band Switching (Patents) Wave-change Switching (Patents) Wave-change Switching (Patents) Wave-training (Patents) Wired-Wireless Systems (Patents), 235, 350, 5 World Physics in Relation to Wireless, Sir Ferror 	1, 134 134 134 134 134 134 134 134			

II. INDEX TO AUTHORS

BAGGALLY, W	65, 413	NORDLOHNE, P. J. H. A 186
BARCLAY, W. A.	307, 552	OLIVER, D. A
Bell, D. A		PRIECHENFRIED, G 487
	123	RATCLIFFE, J. A 354
Bull, C. S	0	RAYNER, E. H. (I.E.E. Paper)
CALLENDAR, M. V.	480	Schneider, A
COATES, J. F. (I.E.E. Paper)	. 434	SCROGGIE, M. G 477, 527, 606
COLEBROOK, F. M.	4, 69, 657	SEKI, H 12
COOPER, M. F. and PAGE, L. G.	469	SHEARING, G. (I.E.E. Paper) 662
DRABBLE, J. C. W. and YEO, R.A.	648	SMITH, C. H
FISHER, C. B	248, 541	SMITH, SIR F. (I.E.E. Kelvin Lecture) 317
GRIFFITHS, W. H. F.	239, 299	Smyth, C. N 134
HECHT, N. F. S. and CROWTHER, H. L.	596	STARR, A. T 609
Hoar, T. P	. 19	STRAFFORD, F. R. W
HOLLINGWORTH, PROF. J. (I.E.E. Paper)	89	
HOLLMANN, H. E.	430, 484	STRUTT, M. J. O
HORTON C. E. and CRAMPTON, C. (I.	$E.\tilde{E}.$	TURNER, L. B. (I.E.E. Paper) 27
Paper)	. 434	URE, W, GRAINGER, E. J. and CANTELO,
Lyons, C. L.	364	H. R. (I.E.E. Paper) 259
McLachlan, N. W.	375	VON ARDENNE M
MEGAW, E. C. S. (I.E.E. Paper)	142, 197	WHITEHEAD, C. C 78
	, - , ,	

PAGE

III. ABSTRACTS AND REFERENCES

PROPAGATION OF WAVES

- On the Absorption of Short Electric Waves in Ionised Gases, an Attempt to Establish the Existence of the Long Wave Radiation of the Hydrogen Atom.—Betz, p. 93.
- of the Hydrogen Atom.—Betz, p. 95. Field Tests on Radio Communication over Long-Distance Aircraft Routes [including the Reduction of Short-Wave Fading by "Alternate Aerial" Transmission or Reception].—von Handel, Krüger and Plendl, p. 557. Characteristics of Electromagnetic Radiation from Aircraft in Plinkt Fung and Coop a Efe
- Flight.—Rives and Coe, p. 558. The New Views on the Composition of the Atmosphere.—Vercelli,
- p. 38?.
- Atmospheric Conditions and the Kennelly-Heaviside Layer .--

- P. 382.
 Atmospheric Conditions and the Kennelly-Heaviside Layer.— Colvell, p. 28.
 Attenuation of Over-Land [and Over Land-and-Water Combina-tions] Radio Transmission in the Frequency Range 1.5 to 3.5 Megacycles per Second.—Anderson, p. 439.
 Effects of the Aurora Borealis [on 40-Metre Band Reception in Pennsylvania]—Skitzki, p. 31.
 The Aurora and World Space Echoes [Suggestion of Long Bands of Particles from the Sun].—Dostal, p. 296.
 "Blanketing" Effect of Aurora and of Electric Charges in the Clouds due to Intense Summer Heat.—Ogilvie, p. 614.
 Auroras : see also Echoes, and under "Atmospherics and Atmos-pheric Electricity."
 Measurements of Attenuation, Fading, and Interference [by Atmospherics] in South-Eastern Australia, at 200 Kilocycles per Second.—Munro and Green, p. 559.
 [Australian] Radio Research Board : Fourth Annual Report (for Year ended 30th June, 1932) [Fading : Lateral Deviation of Sky Wave on Broadcasting Frequencies : Directional Properties of Short Horizontal Aerials : Atmospherics, etc.], p. 265.
 Direct-Ray Broadeast Transmission [and the Prediction of Field Strengths at Distances up to 2000 Kilometres for Wavelengths from 60 to 2.000 Metres].—T. L. Eckersley, p. 29.
 Comparative Field Strengths given by Long and Short Broadcast Waves [550-1450 kc/s].—Byrne, p. 206.
 Note on the Field Intensity of the Marconi Broadcasting Station erected at Warsaw.—T. L. Eckersley, p. 113-114.
 Periodic Variations of the Field Strengths of Broadcasting] Radio Stations [at Short Distances].—Eppen, p. 342.
 Sheath Grounds Affect Travelling Waves in Cables.—Beck, p. 387.
 Travelling Wave Voltages in Cables.—Brinton, Buller and Rudge, p. 616.
 Report on the Tests in the Punkwa Caves and Tunnels.—Fritsch,

- Report on the Tests in the Punkwa Caves and Tunnels .- Fritsch, p. 558.

- Report on trests in the Funkwa Caves and Funkes.—Pritsch, p. 558.
 Symposium on Climatic Cycles [Tree Ring Records, Periodicity in Solar Variation, the Nature of the Solar Cycle, Correlation of Sedimentary and Climatic Records], p. 321.
 Some Results of Further Studies in the Correlation of Cosmic Phenomena with Radio Intensities. as measured at the Perkins Observatory.—Stetson, p. 615.
 The Applicability of the Resonance Method to the Measurement of Dielectric Constants of Aqueous Solutions.—Jetewski, p. 207.
 Measurements of Dielectric Losses in Castor Oil [Confirmation ot Debye's Formulae for Anomalous Dispersion and Absorption, for Wavelengths 200-2 000 Metres.—Stock, p. 93.
 Dielectric Polarisation in Solid Bodies.—Errera, p. 498.
 Characteristics of Differential Systems, and the Propagation of Waves.—Levi-Civita, p. 321.
 The Wave Equation on the Riemannian Logarithmic Surface : On a Problem in the Diffraction of Waves.—Soboleff : Volterra,

- Volterra, a Problem in the Diffraction of Waves .-- Soboleff : p. 150.
- p. 100. Phenomena of Diffraction at Small Spheres in the Neighbourhood of Foci of Convergent Spherical Waves.—Möglich, p. 616. The Theory of Critical Opalescence in the Diffusion of Light [Dis-crepancies between Observed Facts and the Calculations of Einstein and of Ornstein and Zernicke: a New Theory].—

- Einstein and of Ornstein and Zernicke: a New Theory].--Rocard, p. 93. Discussion of Some Asymptotic Expansions in the Theory of the Vertical Electric Dipole.--Murray, p. 616. Optical Dispersion: Quantum Theory of Dispersion. [Surveys]. --Korff and Breit: Breit, pp. 31 and 150. Dispersion of Light caused by Sound Waves.--Debye, p. 167. Investigations of Dispersion [in Liquids] with Undamped Ultra-Short Waves.--Seeberger, p. 207. Short-Wave Dispersion [in Polar Liquids].--Luthi, p. 321. A Study of the Intensity Variations of Doyncoming Wireless Waves [Lateral Deviation and Fading].--Ratcliffe and Pawsey, p. 384. The Influence of the Earth in Radio Communication.--Smith-Rose, p. 497.

- n. 497.
- Radiation from Antennae under the Influence of the Earth's Properties. E.-Radiation into the Earth.-Strutt, p. 624 Earth : see also Ground.
- Earth : see also Ground. The Characteristics of a Deep Focus Earthquake : a Study of th Disturbance of February 20, 1931.—Scrase, p. 208. Some Remarks on the [Japanese] Earthquake of 2nd March, 1933.-Brazier and Génaux : Maurain, p. 267. a Study of the

- Abnormally Good Reception from W3XAL (16.87 m) in England on
- Eve of Californian Earthquake, p. 321. Periodic Components in Love Waves [from the 1922 Formosa Earthquake Records].—Labrouste, p. 561. Considerations for the Explanation of World Space Echoes, the Aurora and Magnetic Disturbances. Part I.—Dostal: Störmer, p. 31. n 31
- Polarisation of Echoes from the Heaviside Layer [Sense of Polarisa-
- tion of Split-Echo Rays].—T. L. Eckersley, p. 386. Echo Measurements on the Ionised Layers of the Atmosphere [on Six Rapidly Changed Wavelengths between 40 and 1000
- Metres].—Goubau, p. 383. A Method of Automatically Recording Echoes from the Ionosphere [using a Cathode-Ray Oscillograph and capable of recording Simultaneous Tests on Several Wavelengths].--Goubau and Zenneck, p. 320. Recording Wireless Echoes at the Transmitting Station.—Ranzi,
- p. 559.
- p. 539.
 P. 539.
 Recording Wireless Echoes at the Transmitting Station.—Mitra and Rakshit: Watson Watt and Bainbridge-Bell, p. 386.
 The Effect of the Sun's Eclipse on Radio Waves [Facsimile Observations on about 35 Metres and Aural on 30 Metres: Effect of Electronic Shadow Found].—Alexanderson, p. 91.
 New Radio Field Stations; Measurements during Eclipse.—Bureau of Standards p. 2000.
- of Standards, p. 30. Measurements of Ionisation in the Kennelly-Heaviside Layer during

- Measurements of Ionisation in the Kennelly-Heaviside Layer during the Solar Eelipse of 1982.—Henderson, p. 264.
 Fading and Signal-Strength Measurements taken during the Solar Eclipse of August 31st, 1932.—Henderson and Rose, p. 264.
 Observations of the Effective Height of the Kennelly-Heaviside Layer and Field Intensity during the Solar Eclipse of August 31st, 1932.—Kenrick and Pickard, p. 386.
 Eclipse Cinematography [Technique, and Importance as Aid in Determining Exact Times of Contact and Duration].—Korfi, p. 265.
- p. 265. Photometric

- p. 265.
 Photometric Study of the Partial Eclipse of the Moon, 14th September, 1932 [and Deductions regarding the Ozone and Heaviside Layers].—Link, p. 150.
 Photometric Theory of Lunar Eclipses [Leading to the Deduction of an Absorbing Layer at about 150 Kilometres].—Link, p. 207.
 The Eclipse of the Sun of 31st August, 1032, and the "Sounding" by Atmospheric Parasites.—Lugeon, p. 92,
 Observations in Transmission during the Solar Eclipse of August 31st, 1932.—Martin and McCuskey, p. 387.
 Continuous Kennelly-Heaviside Layer Records of a Solar Eclipse [with Suggestions of a Corpuscular Effect on Appleton Layer].— Mimno and Wang, p. 386.

- fwith Suggestions of a Corpuscular Effect on Appleton Layer]— Mimno and Wang, p. 386.
 Effect of the Solar Eclipse on the Ionosphere.—Mitra, Rakshit, Syam and Ghose, p. 614.
 Observations on the Kennelly-Heaviside Layers during the Solar Eclipse of 31st August, 1832 [Investigation of "Corpuscular Eclipse" Effects on 60-Metre Wave Reflection].—Paul, p. 320.
 Radio Observations on the Upper Ionised Layer of the Atmosphere at the Time of the Total Solar Eclipse of August 31st, 1032.— Rose, p. 264.
 An Effect of the Recent Solar Eclipse on the Ionised Layers of the Upper Atmosphere [supporting Ultra-Violet Light as Ionising Agency for Lower Layer].—Schafer and Goodall, p. 91.
 The Photometry of Solar Eclipse Phenomena.—Sharp and others, p. 561.

- The Photometry of Solar Eclipse Phenomena.—Sharp and others, p. 561. Amateur Observations during the Total Eclipse of the Sun.— Woodward, p. 149. Radio Observations during the Total Solar Eclipse of Aug. 31st [and the Nature of the Ionising Agency], p. 30. Ionisation during Lunar Eclipses, p. 30. Eclipse : see also under "Atmospherics." Calculation of the Electromagnetic Field of an Alternating Current in a Space with a Plane Boundary Surface.—Fock, p. 616. An Electron Orbit in the Magnetic Equatorial Plane of the Earth. —Swann, p. 31.
- -Swann, p. 31. Ellipsoidal Functions and Their Application to Some Wave

- Bilinsoidal Functions and Their Application to Some Wave Problems.—Hanson, p. 580.
 The Occurrence of "Evening Concentration" in the Appleton Layer.—Paul, p. 320.
 A Preliminary Investigation of Fading in New South Wales.
 Studies of Fading in Victoria: a Preliminary Study of Fading on Medium Wavelengths at Short Distances. 3. Studies of Fading in Victoria: Observations on Distant Stations in which no Ground Wave is received.—Green and Baker: Cherry and Martyn: Cherry, p. 385.
 Selective Fading Phenomena and Height Measurements of the Ionosphere [Fictitious Heights liable to be obtained by the "Pulse" and Other Systems].—von Handel and Plendl, pp. 383 and 497.
- and 497.
- and 487. Investigation of Selective Polarisation Changes and Fading, by Frequency-Change and Pulse Transmissions.—von Handel, Krüger and Plendl, p. 558. Fading and Night Distortion [Observations on Colombo Station],
- p. 30.

Propagation of Waves.

- Fading : see also Australia, Downcoming, Polarisation. Fermat's Principle [Theoretical Discussion].—Natanson, p. 494. Electromagnetic Field at a Distance from a Transmitter [General Discussion: Watson, Austin-Cohen, and Eckersley Formulae: Madrid Conference Sub-Committee Reports], p. 439.
 A Field Intensity Meter [using a Modified Superheterodyne Circuit].

- A Field Intensity Meter [using a Modified Superheterodyne Circuit]. —Brown and Koehler, p. 48.
 Portable Long Wave Testing Apparatus [Field-Strength Measuring Set].—de Coutouly, p. 223.
 A Note on an Automatic Field Strength and Static Recorder.— Mutch, pp. 222-223.
 Measurements of the Electromagnetic Radiation from Aerials [Field-Strength Measuring Set for Motor-Car Transport: Charis of Poste-Parisien and Radio-Paris: Results over Sea, with Comparison of Austin Formula and Madrid Conference Curves: P. P. Eckersley's Indirect Night-Field Rule].—David, p. 439.
 Field-Strength Measuring Set for Ground and Sky Waves, and Some Results of Practical Tests.—Green and Wood, pp. 574-575.
 Propagation Characteristics of High-Frequency [Short] Radio Waves, and a Method of Calculation of Their Field Strengths.—
- Waves, and a Method of Calculation of Their Field Strengths.-
- Namba, p. 149. A Method of Calculation of Field Strengths in High-Frequency Transmission.—Namba and Tsukada, pp. 149 and 560. The Contribution of Radiotelegraphy to Geophysics, p. 382. The Optical Behaviour of the Ground for Short Radio Waves.

- Feldman, p. 497. Ground : see also Earth, Soil. Cyclones, Anticyclones, and the Kennelly-Heaviside Layer.---Colwell, p. 387.
- Measurements of the Height of the Heaviside Layer.—Elias, von Lindern and de Vries, p. 496. Note on a Multifrequency Automatic Recorder of Kennelly-Heaviside Layer Height [and the Existence of Three Layers].— Gilliland, p. 439.
- Ginnard, p. 459.
 Kennelly-Heaviside Layer Measurements on the Byrd Antarctic Expedition, 1929-30.—Hanson, p. 265.
 Records of the Effective Height of the Kennelly-Heaviside Layer [Frequencies 2 050 and 4 095 kc/s].—Kenrick, p. 496.
 A New Modulator for Use in Kennelly-Heaviside Layer Recording. —Minno, Wang and King, p. 320.
 Double-Refraction Effects in the Kennelly-Heaviside Layers.— Minno and Wang, p. 438.
 A Balanced Receiving Circuit for Kennelly-Heaviside Layer Observations [Avidance of Parabasis by Direct Badiation].—

- A Balanced Receiving Circuit for Reineny-neavisitie Layer Observations [Avoidance of Paralysis by Direct Radiation].— Mimno and Wang, p. 439. Heaviside Layer Height Measurement: A Pulse-Generating Circuit using the Intermittent Discharge through a Gas-Filled Triode.—Verman and Mahomed, p. 497.

- Triode.--Verman and Mahomed, p. 497. Measurements on the Kennelly-Heaviside Layers by a Continuously Recording Method.--Wolf, p. 268. Heaviside Layers: see also Atmospheric, Ionisation, Ionised, Ionosphere, Long Wave, Magneto-Ionic, Outer Atmosphere, Propagation, Reflecting, Reflection, Short Wave, Stratosphere, Temperature, Upper Atmosphere. The High-Frequency Discharge [and the Formation of "Plasmoids" at Mid-Points of the Internodes of the Standing Waves].--Chenot: Wood, p. 498. The High-Frequency Discharge in Gases [and the Effects of a Magnetic Field].--Jonescu and Mihul, p. 439. Ionisation of Air and Hydrogen in the High-Frequency Discharge.--Jonescu and Mihul, p. 485.

- Jonescu and Mihul, p. 498. High-Frequency Discharge, Fields: see also Ionised. Theory of the Transmission of Waves in an Ionised Gas in which there is a Horizontal as well as a Vertical Gradient.—Eckersley, p. 613.
- A New Method of Calculating the Hypo-central Depth.-Caloi, p. 561.

- p. 301.
 Investigations on Space Charges in Ice [and Their Effect on the Dielectric Constant].—Oplatka, p. 616.
 Refraction of Infra-Red Rays [Ships detected 6 Miles beyond Horizon].—Macneil, p. 561.
 On the Bearing of the Natural Infra-Red Oscillations of Materials on Their Dielectric Losses.—Czerny and Schottky, p. 31.
 Interaction of Radio Waves [in the Propagating Medium].—Tellegen, np. 437 and 558

- Interaction of Radio Waves [in the Propagating Medium].—Tellegen, pp. 437 and 558.
 The Properties of the Interference of Widely Divergent Pencils of Light Rays [and the Polarisation in the Interference Field of Two Pencils].—Wawilow and Brumberg, p. 387.
 The Interference Pattern of Three Carrier Waves [Investigation of Three Transmitters each radiating the Same Speech Message with a Frequency Separation of about 7 Kilocycles/Second].— Ladner and Wassell, pp. 207 and 267.
 Causes of Ionisation in the Upper Atmosphere.—Ranzi, p. 28.

- Causes of Ionisation in the Upper Atmosphere.—Kanz, p. 28.
 Evidence of a Minor Effect of Corpuscular Radiation on Atmospheric Ionisation.—Burton and Boardman, p. 149.
 Weekly Measurements of Upper-Atmospheric Ionisation [Variation in Region E over Sunspot Cycle : Thunderstorms as Subsidiary Ionising Agency: etc.].—Appleton and Naismith, p. 494.
 Ionisation in the Upper Atmosphere at about 200 km above Sea Level.—Hulburt, p. 496.
 Ionisation Density and Critical Frequency.—Tonks, p. 559.

- Properties of Ionised Gases in High Frequency Fields.-Gutton, p. 440. The Propagation of Electrical Oscillations along a Tube containing
- an Ionised Gas.—Gutton and Chenot, p. 266. Ionised Gases in the Magnetic Field; Pressures less than 10⁻³ mm Hg [and the Effect of Water Vapour].—Jonescu and Mihu!,
- p. 92. Just and Magnetic Field: Pressures greater than 10-3 mm Hg.-Jonescu and Mihul, p. 93.

- mm Hg.—Jonescu and Mihul, p. 93.
 The Absorption of Energy in Ionised Gases.—Jonescu and Mihul, p. 264.
 The Faraday Effect in Ionised Gases for Waves of Length 4 cm.— Keck, p. 207.
 On the Absorption of the Debye-Falkenhagen Relaxation Force in a Neutral, Partially Ionised Gas.—Plasma, Kennelly-Heaviside Layer.—Niessen, p. 28.
 The Charge of Spherical Particles in an Ionised Field.—Pauthenier and Moreau-Hanot, p. 150.
 Ionised Fields, Gases : see also High-Frequency.
 A Comparison of the Frequency-Change and Group-Retardation Methods of Measuring Ionised-Layer Equivalent Heights...-Naismith, p. 264.
 General Theory of the Propagation of Radio Waves in the Ionised
- Naismith, p. 264. General Theory of the Propagation of Radio Waves in the Ionised Layer of the Upper Atmosphere.—Namba, pp. 149 and 497. The Geophysical Significance of Radio Measurements of the Ionised Layer [and a Discussion of Bartel's Correlation Methods and Tests for Harmonic Components].—Tuve: Bartels, p. 265. Wireless Studies of the Ionosphere [including a Section on the Magneto-Ionic Theory and an Extension of the Lorentz Dis-persion Theory de Appleton p. 20.

- Magneto-tonic Theory and an Extension of the Lorentz Dis-persion Theory].—Appleton, p. 30. The Ionosphere—Professor Appleton's Address to the Royal Society.—Appleton, p. 494. Fine-Structure of the Ionosphere.—Appleton, p. 558. The Ionosphere as a Doubly-Refracting Medium [Split Echoes due to Magneto-Ionic Double Refraction].—Appleton and Builder, p. 262.
- Continuous Measurements of the Virtual Heights of the Ionosphere
- Continuous Measurements of the Virtual Heights of the Ionosphere [on a Frequency of 4 100 kc/s].—Gilliand, p. 614. The Generation and Reception of Wireless Signals of Short Dura-tion [for Investigation of Ionosphere].—Herd, p. 263. Studies of the Ionosphere and Their Application to Radio Trans-mission [Measurements of Critical Frequencies : the F Region composed of Two Layers by Day : Skip Distances as Absorption, not Penetration, Phenomena].—Kirby, Berkner and Stuart, p. 438. 438.

- 438. Measurements of Echoes from the Ionosphere at the Summer Solstice [1933: Broadcast and Short Waves].—Mögel, p. 613. Researches on the Distribution of Ionic Density in the Ionosphere and on ifts Variations.—Ranzi, p. 384. An Automatic Recording Method for Wireless Investigations of the Ionosphere fand a Discussion of Some Results: Thunder- and Shower-clouds as the Cause of Abnormal E-Layer Ionisation].—

- Shower-clouds as the Cause of Abnormal E-Layer Ionisation].— Ratcliffe and White, p. 495. Fine-Structure of the Ionosphere.—Ratcliffe and White, p. 559. Characteristics of the Ionosphere.—Verman, p. 614. The Ionosphere.—Watson Watt, p. 559. Ionosphere Investigations in High Latitudes.—Appleton, Naismith and Builder, p. 613. Kennelly-Heaviside Layer: see Heaviside Layer. Lateral Deviation : see Downcoming.

- Lateral Deviation : see Downcoming. Theoretical Investigation on Currents through the Bridge and

- Inderial Deviation 1: see Powher System.—Ataka, p. 171.
 Theoretical Investigation on Currents through the Bridge and through the Ends of a Lecher Wire System.—Ataka, p. 171.
 Radio-Frequency Transmission Lines: Ellipse Diagram of a Lecher Wire System: Application of Circle Diagram to Transmission Lines.—Roder : Hikosaburo: Creedy, p. 321.
 Luminou Discharge between Lecher Wires in a Partially Evacuated Tube. Hershberger, Zahl and Golay, p. 498.
 Leeher Wires: see also under ' Measurements and Standards.''
 The Depolarisation of Light diffused by a Uniaxial Crystal when the Optical Axis is Parallel to the Diffused Ray. Experimental Study and Theoretical Considerations.—Cabannes, p. 387.
 Light Intensity at Different Depths in Lake Water [down to 70 Feet: Exponential Intensity Variation for Some Wavelengths only: Calculation of Absorption Constants].—Erikson, p. 387.
 Light Rays and Wave Surfaces in General Anisotropic Bodies.—Frank, p. 208.
 Line Oscillations—" Tuned Power Lines" [101 km Telephone Line with Ground Return set into Resonance Oscillation at 940 Crycles/Scond].—Marro, p. 616.

- Cycles/Second].---Marro, p. 616. On Linear Systems with First-Order Partial Derivatives with Two

- On Linear Systems with First-Order Partial Derivatives with 1wo Variables.—Carleman, p. 616. Long Wave Transmission, Treated by Phase Integral Methods.— T. L. Eckersley, p. 28. Remarks on the Propagation Law for Long Electric Waves and the Action of the Heaviside Layer [with a New Interpretation of the Austin Formula].—Noether, p. 381. Theory of the Propagation of Low-Frequency [Long] Waves [Change from Metallic to Dielectric Reflection, etc.].—Yokoyama and Namha n. 30
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Propagation of Waves.

The Discontinuous Nature of Love Waves.--Coulomb, p. 616. Propagation of Waves: Work of Special Committee at Lucerne

- [Qualifying and Amplifying Madrid Committee's Reports], p. 560. The Propagation of Waves: an Account of Work carried out at Madrid [Field Intensities for 1 kw_Radiated, Wavelengths
- Madrid [Field Intensities for 1 kw Radiated, Wavelengths 150-2000 Metres: Limiting Ratio of Fields of Two Stations on Same Wavelength], p. 319. Propagation of Waves of 150 to 2000 Kilocycles per Second (2000 to 150 Metres) at Distances between 50 and 2000 Kilo-meters [Madrid Sub-Committee Graphs of Average Data].— van der Pol, Eckersley, Dellinger and le Corbeiller, p. 560. The Surface of Waves in a Liquid submitted to the Action of a Magnetic Field.—Cotton p. 321

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- Malzev, p. 561.
- The Theoretical Frequency Distribution of Photographic Meteors .---Millman, p: 207.
- The Ionising Effect of Meteors in relation to Radio Propagation .--Skellett, p. 207.
- Meteors cause Reflection of Short Wave Radio Signals.—Skellett : Schafer and Goodall, p. 92. Observations of Kennelly-Heaviside Laver Heights during the Leonid Meteor Shower of November, 1931.—Schafer and Goodall, p. 207.
- Meteors; see also Winds, and under "Atmospherics." Direct Measurement of the Gravitational Effect of the Moon [Unexplained Lag, larger than Computed Effect of Sun].--
- Hartley, p. 387. Further Results in the Study of Apparent Variations of the Vertical with the Hour-Angle of the Moon.—Stetson : Loomis and
- Stetson, p. 615.
- Moon : see also Periodicities
- The Outer Atmosphere of the Earth [A Survey].—Hulburt, p. 32. The Effect of High-Tension Overhead Lines on the Propagation of Electromagnetic Waves.—Zuhrt, p. 206. Propagation of High-Frequency Currents along Overhead Power Lines affected by Short-Circuits or Faults in Insulation.—Fallou, p. 440.

- p. 440.
 The Absorption of Oxygen in the Ultra-Violet [and the Existence of an O, Molecule].—Herman, p. 498.
 Study of Atmospheric Ozone by a Rapid Method of Visual Photometry.—Gauzit, pp. 92 and 560.
 Vertical Distribution of Ozone in the Atmosphere.—Götz, Dobson and Meetham, p. 560.
 The Magnetic Properties of Liquid Ozone.—Lainé, p. 387.
 Ozone and the Sunspot Cycle [Latest Observations Not Confirming a Correlation].—Fowle, p. 615.
 The Bright and Dark Fringes on the Edges of the Penumbra thrown by an Opaque Body illuminated by a Large Source of Light.—Wolfers: Demetrovic, p. 31.
 Some Common Periodicities in Radio Transmission-Phenomena [Solar Rotation Period and Its Prominent Third Harmonic : Lunar Period, with Prominent Second Harmonic suggesting a Kennelly-Heaviside Layer Tidal Effect].—Kenrick and Pickard, p. 265. p. 265.
- The Influence of the Earth's Magnetic Field on the Polarisation of Sky Waves.—Baker and Green, p. 385. The Limiting Polarisation of Downcoming Radio Waves Travelling Doliquely to the Earth's Magnetic Field.—Baker and Green, p. 614.
- The State of Polarisation of Sky Waves : Height Measurements of the Heaviside Layer in the Early Morning [Waves of Broadcast Frequencies].—Green, p. 385. The Magnetic Rotation of the Plane of Polarisation of Electro-
- magnetic Waves in Ionised Gases [Experimental Confirmation of Theory].--Keck and Zenneck, p. 92. The State of Polarisation of Downcoming Wireless Waves of Medium
- Length [and the Cause of Rapid Fading] .- Ratcliffe and White p. 559.
- On Radiometer Action and the Pressure of Radiation .- Bell and
- On the Pressure of Radiation at Refraction.—Bellia, p. 208. On the Pressure of Radiation at Refraction.—Bellia, p. 208. The Appleton-Hartree Formula and Dispersion Curves for the Propagation of Electromagnetic Waves through an Ionised Medium in the Presence of an External Magnetic Field. Part I: Curves for Zero Absorption.—Mary Taylor, p. 263. Propagation of 150.000 has come Distances of 50.2000

- Curves for Zero Absorption.—Mary Taylor, p. 203. Propagation of Waves of 150-2000 kc/s over Distances of 50-2000 km.—van der Pol, p. 382. Remark on a Paper by Murray and One by van der Pol and Niessen on the Propagation of Electromagnetic Waves.—Niessen, p. 382. Results of the Third [Polish] Investigations on the Propagation of Intermediate [200-50 m] and Short[50-10 m] Waves.—Sokolcow and Bruerski n. 292 and Bylewski, p. 386.

The Propagation of Electromagnetic Waves—Account of the Facts already Acquired; Synthesis of Ideas and Theories.—Labbat, p. 440.
Propagation of Electromagnetic Waves [over the Surface of a Conductive Earth: Revival and Amplification of Vaschy's Treatment (1925)].—Pomey, p. 615.
Pulse Generator using Cold-Cathode Neon Discharge Tube and giving 100-Microsecond Pulses.—Verman, p. 614.
Some Applications of the Reciprocity Theorem in Radio Telegraphy. —Graffin, p. 81.

- -Graffi, p. 31. The Reflecting Layers of the Upper Atmosphere [and Changes in Barometric Pressure].--Colwell and Myers, p. 437. Measurements of the Reflection at the Heaviside Layer.--Elias
- and von Lindern, p. 206. and von Lindern, p. 206. Experimental Researches on the Total Reflection of 18-cm Hertzian Waves [and the Study of a Radiometer suitable for these Waves]. --Beauvais, pp. 150, 440, 494, 558. Metallic Reflection. IV. Propagation of Electromagnetic Waves along Curved Wires.-Ebeling, p. 498. The Reflection of Light at a Surface Covered by a Monomolecular Film --Strachan 908

- Film—Strachan, p. 208. Phase Changes at Reflection by Very Thin Metallic Layers.— Rouard, pp. 208, 440. The Reflection of Plane Wave Pulses from Plane Parallel Plates.—
- Muskat, p. 616. The Propagation of Electromagnetic Fields along Rivers [Tests along the Danube in Flat and Mountainous Regions].—Fritsch, p. 319.
- The Scattering of Light [and the Effect of Particle Size].-Bancroft
- The Scattering of Eight (and the Ellect of Faiture Size).—Baltfort and Gurchot, p. 267. The Scattering of Light in Very Clouded Media.—Fabrikant, Ginsburg and Pulver, p. 387. On the Scattering and Absorption of [Plane] Electromagnetic Radia-tion by a Small Sphere.—Beck and Wenzel, p. 616. The Screening of the Magnetic Field of Cylindrical Coils.—Hillers,
- p. 281.
- The Theory of the Interpretation of Seismic Travel-Time Curves in Horizontal Structures.—Slichter, p. 150. The Theory of Refraction Shooting [of Seismic Waves].—Muskat, p. 321.
- p. 662. The Transmission of Seigmic Waves [Deductions from the Santiago Data].—Neumann, p. 616. Electromagnetic-Wave Prospecting in U.S.S.R. [and the Theory of Propagation in Semi-Conducting Media].—Petrowsky, p. 498. Electromagnetic Shielding at Radio Frequencies.—King, p. 206.

- Experiments on Electromagnetic Shielding at Frequencies.—King, p. 206. Experiments on Electromagnetic Shielding at Frequencies between One and Thirty Kilocycles.—Lyons: King, p. 403. North Atlantic Ship-Shore Radiotelephone Transmission during 1930 and 1931 [Analysis of Short-Wave Data: Field Strength Contour Diagrams, etc.].—Anderson, p. 206. The Apparent Velocity of Short Radioelectric Waves.—Stoyko and Louvet a 427.

- The Apparent Velocity of Short Radioelectric Waves.—Stoyko and Jouaust, p. 437.
 Anomalies in the Propagation of Short Radioelectric Waves [Abnormally Long Path Time for Annapolis Time Signals received in France].—Stoyko and Jouaust, p. 437.
 Short-Wave Transmission to South America [Survey of Transmission Conditions: Absence of Seasonal Effect: Characteristics of Atmospheric Noise, etc.].—Burrows and Howard, p. 206.
 Studies in Radio Transmission [Short-Wave Echo, Field Strength and Faccimite Measurements].—T. L. Eckersley, p. 29.
 Some Characteristics of Short-Wave Propagation [especially Long-Distance Reception of a Single. Very Hirb-Angle Rayl.—Holling-

- and Facsimile Méasurements].—T. L. Eckersley, p. 29.
 Some Characteristics of Short-Wave Propagation [especially Long-Distance Reception of a Single, Very High-Angle Ray].—Hollingworth, pp. 91, 206, 319.
 Experimental Contribution to the Study of the Propagation of Short Waves [based on Paris-Buenos Ayres and Paris-New York Services].—Maire, p. 404.
 Transoceanic Reception of High-Frequency [Short-Wave] Telephone Signals (and the Correlation of Magnetic Activity and Signal Strength].—Morris and Brown, p. 230.
 Angle of Elevation of Short-Wave Rays.—Walmsley, p. 91.
 Short-Wave Broadcasting in the Dutch East Indies.—Kuyck, p. 497.
 The Electrical Properties of Soil for Alternating Currents at Radio Frequencies.—Smith-Rose, p. 382.
 Transoceanic [Short-Wave] Radio and Solar Activity.—Brown : National Broadcasting Currents and Solar Influences on Radio Transmission [Survey].—Appleton, p. 265.
 Solar Influences on Sound in the Atmosphere: a Suggested Explanation [of the Observed Absorption more than Twenty Times as great as the Calculated].—Rocard, p. 321.
 The Relation between the Resolving Power of a Spectroscope and the Principle of Uncertainty.—Goldman, p. 267.
 Small Sphere : see Diffraction, Scattering.
 Standing Light Waves; Repetition of an Experiment by Wiener, using a Photoelectric Probe Surface—Ives and Fry, p. 335.
 Effect of Storms on Radio.—Colwell and Myers, p. 321.
 Radio Transmission from the Stratosphere, during Piccard's Ascent, p. 92.

- p. 92.
- On Energy Effects in the Troposphere produced by Pressure Variations in the Stratosphere.—Ertel, p. 266. Clouds in the Stratosphere.—Störmer, p. 497.

Propagation of Waves.

Progress in the Studies of Cosmic Correlations with Radio Reception at the Perkins Observatory [Closer Inverse Correspondence of Radio Reception with Sunspot Numbers—Closer than with Ultra-Violet Radiation : Correlation with Lunar Altitudes].— Stetson, p. 265.

- Suction, p. 265. Sun Spots and Radio Reception.—Stetson, p. 265. "Those Sunspots" [Choice of Working Waves for Short-Wave Services].—Alway, p. 320. Sunspots : see also under "Atmospherics and Atmospheric Elec-tricity."

Superposition of Two Modulated Radio Frequencies [Treatment applicable to Direct and Reflected Beams].—Roder, p. 210. The Diffraction of Light by [Supersonic] Elastic Waves.—Lucas,

- p. 150.
- Optical Properties of Solid and Liquid Media submitted to Supersonic Elastic Vibrations.—Lucas and Biquard, p. 31. Some Experiments on the Diffraction of Light by Supersonic Waves.

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 The Change of Form undergone by Surges as a result of Corona Loss.—F. Voerste, p. 387.
 The Damping of Surges on H.T. Lines [Higher Values than those calculated from Skin Effect, and Their Causes].—Flegler and Röhrig, pp. 440 and 616.
 Distant Television Reception : Multiple Images due to Propagation Effects.—Bodroux and Rivault, pp. 572-573.
 The Temperature of the Upper Atmosphere deduced from Day/ Night Change of Height of Absorption Layer for Auroral Light.— Angenheister, p. 540.

Angenheister, p. 560. The Non-Uniform Transmission Line : Corrections.—Starr, p. 31 Linearly Tapered Loaded Transmission Lines.—Arnold and Taylor, p. 150.

- p. 130. Theory of the Propagation of Electrical Energy along Transmission Lines.—Bláha, p. 321. Checking the Behaviour of Ultra-High-Frequency [2- and 5-Metre] Waves: Interesting Transmission Tests using Directive Aerials.
- -Jones, p. 328. Experiments on Ultra-High-Frequency Communications [on 8.2-Metre Wave from Summit of Mt. Fuji].--Nakai, Kimura and Ueno, p. 173.
- The Ultra-Short-Wave Service between Corsica and the Continent.
- In Contra-Short-Wave Service between Corsica and the Continent. ---de Clépoulx, pp. 228-229.
 Some Results of a Study of Ultra-Short-Wave Transmission Pheno-mena [Effect of Reflection Components : Three Reflection Surfaces even in Hill-to-Hill Transmission: Comparison of Methods of Field Strength Measurement : etc.].-Englund, Crawford and Mumford, pp. 318 and 381.
 Propagation Tests with the 1.3-Metre [Ultra-Short] Wave.-Esau and Köhler n. 381.
- and Köhler, p. 381. Absorption and Reradiation of [Ultra-] Short Electric Wayes,-

- Absorption and Reradiation of [Ultra-Short] Onor, License Fountain, p. 327.
 A Study of the Propagation of [Ultra-Short] Wavelengths between, Three and Eight Metres [and an Empirical Ultra-Short-Wave Propagation Formula].—Jones, p. 334.
 Some Characteristics of Five-Metre [Ultra-Short-Wave] Transmission.—Kraus, p. 558.
 "Ultra-Shorts" from the Air [Transmissions from an Aeroplane : Occurrence of Shadows cast by Banks of Cloud or Rain ?].—Morgan, p. 494.
- Occurrence of Snadows cast by Banks of Cloud or Rain (].— Morgan, p. 494.
 Witra-Short-Wave Tests from Summit of Mount Snowdon [Five-Metre Signals to Hoddesdon, Herts, 200 miles away].—O'Heffer-man and Myatt, p. 558.
 Radio-telephone Service between France and Corsica on Ultra-Short Waves.—Picault, p. 31.
 Witra-Short-Wave Propagation [with Methods of Measuring Attenua-tion and Field Strougth . Important Action of Benetian Probatisms
- tion and Field Strength : Important Action of Regular Reflection and of Diffraction : etc.].—Schelling, Burrows and Ferrell, pp. 318 and 381.

- The Propagation of Ultra-Short Waves.—Smith-Rose, p. 148. Notes on Propagation of Ultra-Short Waves below Ten Metres in Length [Empire State Building and Other Transmissions].— Trevor and Carter, pp. 334-335. The Propagation of Ultra-Short Waves through Oil and Water.— Uda and Takao 9 31
- Uda and Takao, p. 81. Experiments with Ultra-Short Waves : Demonstration [on 65-cm Wavelength : including Imitation of Fading].—Yates-Fish, p. 494.
- The Damping of [Ultra-] Short Waves by Conductive Walls .---Zuhrt, p. 493, Field Strength Measurements of Ultra-Short Waves from Empire

- Fleid Strength Measurements of Ultra-Short Waves from Empire State Building, p. 207.
 Recent American Amateur Results on Ultra-Short Waves (56 Megacycle Band), p. 148.
 Experiments on the Propagation of Ultra-Short and Micro-Waves in Tunnels [the Shafts and Galleries of Mines and a Concreted Tunnel].—Arenberg and Peicikov, p. 558.
 Considerations on the Propagation of Ultra-Short and Micro-Waves. —Pession, p. 493.

- Ditra-Shori, p. 490. Ultra-Shorit and Micro-Waves : see also Very Short. Present Knowledge of the Upper Atmosphere.—Appleton, p. 30. A Survey of the Physics of the Upper Atmosphere.—Bartels, pp. 92 and 262.

Discussion on Papers by Bartels and Rukop on the Upper Atmo-sphere,-Bartels: Rukop: Lassen: Franck, p. 382. The Existence of More Than One Ionised Layer in the Upper

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- 20, and 495.
 New Range Tests with Very Short Waves of 60 Centimetres.— Marconi, p. 615.
 Progressive Periodic Waves at the Surface of Water in a Shallow Container [Verification of Kelvin's Formula].—Baurand, p. 387.
 Wireless Reception and the Weather [Correlation between Baro-metric Pressure and Strength of WCAU Signals at Paisley, Renforwshirel p. 391.
- Renfrewshire], p. 321. The Influence of the Weather on the Propagation of Radio Waves.-
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ATMOSPHERICS AND ATMOSPHERIC ELECTRICITY

- Electrical Properties of the Atmosphere in the Neighbourhood of Flying Aircraft [Marked Stratification of Atmospheric Space Charge at and just above Cloud Level: Possibility of using Electrical Phenomena as an aid to Height Estimation in Blind

- Electrical Phenomena as an aid to Height Estimation in Blind Flying].—Rose, p. 442. An Extremely Simple Method of Periodogram Analysis [taking One-Third the Time taken by Correlation Periodogram : Cal-culations made on ordinary Adding Machine].—Alter, p. 323. Practical Application of Periodogram Analysis.—Sandström : Lind-quist, p. 389. Principles of Statistical Analysis Occasionally Overlooked [Appli-cation to Cosmic Ray Data].—McNish, p. 499. The Effects on Human Beings of Atmospheric Electrical Phenomena and Meteorological Influences.—Chorus and Levi, p. 269. Papers on Atmospheric Electricity and Terrestrial Magnetism, at the International Electricity Congress, Paris, pp. 94 and 151 (two). (two).

- Weather Forecasting by Atmospherics.—Ashwin, p. 323. Noise Intensity due to Atmospherics, Measured at Different Parts of the Broadcast Spectrum.—Byrne, p. 441. On the Rapid Variation of Atmospherics at Sunrise [and Lugeon's "Sounding" of the Upper Atmosphere].—Bureau : Lugeon, p. 440.

- "Sounding" of the Upper Atmosphere].—Bureau: Lugeon, p. 440.
 Probability Ideas applied to Radio Communication: the Question of Atmospherics.—Deloraine, p. 441.
 Directional Studies of Atmospherics at High Frequencies.—Jansky, p. 208: see also end of Cosmic, Static.
 Records of Atmospherics [Pic du Midi, Nov. 1931 to Aug. 1932: Lugeon's "Vertical Sounding" of the Atmosphere].—Link: Lugeon, p. 31.
 Sources of Atmospherics observed between England and Australia, using the Cathode Bay Direction Finder —Munro and Huyley.
- using the Cathode-Ray Direction Finder.—Munro and Huxley, p. 82.

using the Cathode-Ray Direction Finder.—Munro and Huxley, p. 32.
Atmospherics in Australia—I. Radio Research Board, Report No. 5.—Munro and Huxley, p. 267.
Atmospherics ["Fulgurs"] in South-Eastern Australia, measured on a Frequency of 200 Kilocycles per Second.—Munro and Green, p. 561.
Solar Rotation and Atmospherics.—Schindelhauer, p. 208.
On the Relation between Atmospherics and Meteorological Elements observed at Okinawa —Yanagimoto, p. 32.
Results in Cinematographic Height Measurements and Proof of an Infra-Red Radiation in the Aurora Borealis (due to Nitrogen rather than to Oxygen].—Bauer, p. 389.
An Auroral Arc at less than 80 km Height above the Earth.—Harang and Bauer, p. 268.
Low Autoras and Terrestrial Discharges.—Beals, p. 561.
Low Altitude Aurora.—Chapman, p. 93.
Auroral Curtains and the Corpuscular Theory.—Störmer, p. 389.
The Morsehoe Aurora.—Hill: Störmer, p. 268.
The Morsehoe Aurora.—Störmer, p. 269.
The Morsehoe Aurora.—Hill: Störmer, p. 261.

The Horseshoe Aurora.—Hill: Störmer, p. 268. The Auroral Spectrum and Its Interpretation.—Vegard, p. 617. Investigations of the Auroral Spectrum during 1921–26 [and Con-clusions regarding Upper Atmosphere].—Vegard, p. 389. The Audibility of the Aurora, p. 323.

Atmospherics and Atmospheric Electricity.

- Aurora : see also Space Charge.
- A Consideration of the Emission of the Auroral Green Light in the Night Sky [Discussion of the Reactions between Oxygen and
- Nitrogen Atoms).—Kimura, p. 33. Attempts and Suggestions towards the Development of Radio-meteorographical Methods [for Sounding Balloons].—Väisälä, p. 151. Ionisation of the Atmosphere and its Biological Effects.—Koller,
- 32. p.
- The Biological Effect of Cosmic Rays.—Lakhovsky: Rivera, p. 34 The Influence of Humidity on the Breakdown Voltage in Air.—

- The Influence of Humidity on the Breakdown Voltage in Air.— Dei, p. 33.
 Spark-Gap Breakdown : Characteristic Properties of the Glow Discharge.—Hellman : Rogowski, p. 209.
 A Fundamental Problem of the Motion of an Electrically Charged Particle in Cosmic Space.—Störmer, p. 268.
 Study of the Electrical Conductivity and Condensation Nuclei on a Voyage to Greenland.—Maurain and Devaux, p. 93.
 Measurement of the Electrical Conductivity of the Air by a Null Method.—Thellier, p. 442.
 Methods of Measuring the Electrical Conductivity and Ionisation of the Air.—Salles, p. 617.
- of the Air.—Salles, **617**. Bead-Corona on Radio Antenna.—van der Pol, **p. 94**. Origin of Gosmic Radiation.—Alfvén, **p. 388**. Energy Loss and Scattering of Cosmic-Ray Particles.—Anderson,

- Energy-Loss and Scattering of Cosmic-Ray Particles.—Anderson, p. 322.
 Cosmic Ray Bursts.—Anderson, p. 323.
 A Self-Recording Cosmic-Ray Electrometer and Depth-Ionisation Curve.—Benade, p. 95.
 Secondary Radiation Produced by Cosmic Rays.—Benade, p. 95.
 Intensity of Cosmic-Ray Ionisation in Western North America.— Bennett, Dunham, Bramhall and Allen, p. 94.
 New High-Altitude Study of Cosmic-Ray Bands and a New Determination of Their Total Energy Content.—Bowen, Millikan and Neher, p. 617.
 Cosmico-Ray Ionisation as a Function of Pressure, Temperature, and Dimensions of the Ionisation Chamber.—Broxon. p. 95.
- Dimensions of the Ionisation Chamber.—Broxon, p. 95. Fluctuations of Cosmic-Ray Ionisation.—Broxon, Merideth and
- Strait, p. 442. The Corpuscular Nature of Cosmic Radiation and the Effect of
- Terrestrial Magnetism.—Clay, p. 209. Variation of Cosmic Radiation with Geographical Latitude and Terrestrial Magnetism.—Clay and Berlage, p. 34. Professor A. H. Compton's Studies of Cosmic Rays.—Compton,
- p. 34.
- Ionosphere Rays Possible as New Name for Cosmic Rays .-- Compton,
- p. 94.
 Progress of Cosmic-Ray Survey.—Compton, p. 94.
 Sea Level Intensity of Cosmic Rays in Certain Localities from 46°
 South to 68° North Latitude.—Compton, p. 152.
 Some Evidence Regarding the Nature of Cosmic Rays.—Compton,
- p. 322.
- p. 322. Nature of Cosmic Rays.—Compton, p. 387. A Geographic Study of Cosmic Rays.—Compton, p. 322. A Positively Charged Component of Cosmic Rays.—Alvarez and

- A Positively Charged Component of Cosmic Rays.—Aivarez and Compton, p. 442. Spectrum of Cosmic Radiation.—Conway, p. 95. Deflection of Cosmic Rays by a Magnetic Field [Positive Results]. —Curtiss, p. 152. Cosmic Rays—What Physicists Have Learned About Them.— Darrow, p. 389. Secondary Effects of Cosmic Radiation.—Fünfer, p. 500. The Variation with Pressure of Ionisation by Cosmic Rays.—Gross,
- The Variation with Pressure of Ionisation by Cosmic Rays .- Gross, p. 34.
- The Dependence of Cosmic Ray Ionisation on Pressure and Tem-perature.—Gross, p. 209. The Absorption of Cosmic Radiation.—Gross, p. 499.
- Journal Variation of Cosmic Rays and Terrestrial Magnetism.— Gunn, p. 94. Cosmic Rays may be born of Neutral Rays from Stars.—Gunn,
- p. 209.
- High-Speed Ions of Stellar Origin [Bearing on Cosmic Radiation]. -Gunn, p. 389. Latitude Effect of Cosmic Radiation.-Hoerlin, p. 562.
- Use of Argon in the Ionisation Method of Measuring Cosmic Rays and Gamma Rays.—Hopfield, pp. 152 and 499. Efficiency of Geiger Counter and Absorption of Cosmic Rays.—
- Jacobsen, p. 95. The Variation of Cosmic-Ray Intensities with Azimuth on Mt. Washington, N.H.—Johnson, p. 388. The Azimuthal Asymmetry of the Cosmic Radiation.—Johnson, pp. 442 and 499.
- The Direction of Cosmic Rays.—Johnson and Street, p. 34. The Variation of the Cosmic-Ray Intensity with Azimuth.—Johnson
- and Street, p. 94. Comparison of the Angular Distributions of the Cosmic Radiation at Elevations 6 280 ft. and 620 ft. Johnson, pp. 388 and 561. Angular Distribution of Low Energy Cosmic Radiation and Inter-
- pretation of Angular Distribution Curves .-- Johnson and Stevenson, pp. 388 and 562. The Asymmetry of the Cosmic Radiation at Swarthmore.—Johnson and Stevenson, p. 562.

- An Interpretation of Cosmic-Ray Phenomena.-Johnson, p. 94. Cosmic Rays Bombard Earth with 40 000 Million Volts [New
- Cosmic Rays Bombard Earth With 40 000 Million Voits [New Estimate]...-Johnson, p. 34.
 Cosmic Rays.—Theory and Experimentation [History and Present-State].—Johnson, p. 152.
 Counting Cosmic Rays.—Johnson and Street, p. 34.
 The Cosmic-Ray Hodoscope and a Circuit for Recording Multiply Coincident Discharges of Geiger-Müller Counters.—Johnson, p. 296
- p. 388.

- The Cosmic Ray Hodoscope.—Johnson and Stevenson, p. 618. Concerning the Production of Groups of Secondaries by the Cosmic Radiation.—Street and Johnson, p. 34. Remarks on the Problem of Cosmic Rays [Generation of "Positive Electrons" by Impact on Matter].—Kallmann, p. 500. Investigations of the Vertical Counter Effect of Cosmic Radiation. Kolberger, p. 162
- -Kolhörster, p. 152. Proposal for a Uniform Notation for Strength of Gaseous Ionisation
- [application to Cosmic Ray Experiments].—Kolhörster, p. 152. The Hardest Cosmic Rays and the Electric Charge of the Earth.
- The Hardest Cosmic Rays and the Electric Charge of the Earth. —Kolhörster, p. 617.
 The Interpretation of the Experimental Determination of the Mean Specific Ionisation of Cosmic Radiation from Comparative Measurements with an Ionisation Chamber and a Counter.— Kolhörster and Tuwim, p. 322.
 The Straight Line Law in Cosmic Ray Coincidences and Its Experimental Validity.—Kolhörster and Tuwim, p. 618.
 Azimuthal Investigation of Cosmic Radiation.—Korff, p. 562.
 Density of Energy in the Universe [Smaller than Cosmic-Ray Energies].—Korff, p. 618.
 Remark on the Variations of Cosmic Ray Intensity at Great Altitudes.—Kulenkampfi, p. 209.
 Magnetic Spectrum of Cosmic Rays.—Kunze, p. 94.
 Magnetic Deviation of Cosmic Rays in a Wilson Cloud Chamber. —Kunze, p. 268.

- -Kunze, p. 268.
- Investigation of Cosmic Radiation in the Wilson Chamber .- Kunze, p. 499. The Latitude Effect of Secondary Electrons due to Cosmic Rays.
- -Langer, p. 268. Cosmic Rays are Photons, Dr. Millikan declares.-Langer : Millikan,
- p. 322.
- "Super-Radium" Supplied Energy for Rapid Cosmic Evolution [Cosmic Rays are Traces of the Radiation emitted Then].---Lemaitre, p. 95. Einstein Backs Lemaitre Idea that Cosmic Rays are Birth Cries.
- -Lemaitre, p. 209. On Compton's Latitude Effect of Cosmic Radiation.-Lemaitre and
- Vallarta, pp. 152 and 209. Analysis of the Absorption Curve of Cosmic Radiation.—Lenz :
- Analysis of the Absorption Curve of Cosmic Radiation.—Left2: Regener, p. 499. X-Rays made as Cosmic Rays plough through Gas [and cause Part of the Charge in an Ionisation Chamber used for Ray Measure-ments].—Locher, p. 209. Expansion Chamber Data on Cosmic-Ray Ionisation.—Locher,
- p. 323.
- On Measurements of Fluctuation in Cosmic Radiation .- Messer-
- schmidt, p. 34. Disintegration of Atoms by Cosmic Rays.—Messerschmidt, p. 388. Cosmic Rays Measured in Stratosphere [100 Times more intense at 18 Kilometres than at Sea Level].—Millikan, Bowen and
- Neher, p. 388. Cosmie-Ray Intensities in the Stratosphere.—Bowen and Millikan,

- Cosmic-Ray Intensities in the Stratosphere.—Bowen and Millikan, p. 442. Millikan and Compton Debate Cosmic-Ray Facts and Theories.— Millikan : Compton, p. 209. The Sun and Cosmic Kays.—Millikan and Neher, p. 268. New Technique in the Cosmic-Ray Field and Some of the Results obtained with it.—Millikan and Neher, pp. 322, 388. Altitude Increases Quantity of Cosmic Rays.—Mott-Smith, p. 94. Airplane Cosmic-Ray Intensity Measurements.—Mott-Smith and Howell, pp. 94, 322 and 561. The Airplane Method of Obtaining Cogmic-Ray Intensity Data.— Howell and Mott-Smith., p. 322. Origin of the Cosmic Rays.—Piccard, p. 34. Study of the Cosmic Rays.—Piccard, p. 34.

- Cosyns, p. 33. Recent Researches on Cosmic Rays.—Piocard : Regener, p. 33. Measurement of Cosmic Radiation in the Stratosphere.—Regener,
- p. 33.

- p. 33.
 Energy of Cosmie Rays.—Regener, p. 209.
 The Energy Current of Cosmic Radiation.—Regener, p. 268.
 The Absorption Curve of Cosmic Radiation and Its Meaning.— Regener, p. 442.
 Cosmic Rays [Exclusively Corpuscular at Sea-Level: Primary Radiation from Outer Space also probably Corpuscular: "Transition Effects" in Absorption Curves Explained].—Rossi, a 298. p. 388.
- p. 666.
 Interaction between Cosmic Rays and Matter.—Rossi, p. 562.
 The Secondary and Tertiary Particles Produced by Cosmic Rays.— Sawyer, p. 618.
 On the Cosmic Radiation [Theory of Origin covering both Hard and Soft Components].—Sevin, p. 33.

Atmospherics and Atmospheric Electricity.

On the Absorption of Cosmic Radiation by the Atmosphere [Support of the Writer's View of Radioactivity of Free Protons as Ionising Agency and Extra-Nuclear Electrons as Agency for Absorption --Sevin, p. 388. Spectrum of Cosmic Radiation.--Skapski, p. 33. Some New Coincidence Measurements on the Cosmic Radiation.-

- Sparks and Pickering, p. 268. Angular Distribution of Cosmic-Ray Particles.—Stearns and Bennett,
- p. 499. Solar Component of Cosmic Rays.—Stearns, Overbeck and Bennett,
- Solar Component of Uosmic Rays.—Stearns, Oversteen and Database p. 95. The Disintegration of Various Materials by Cosmic Radiation.— Steinke, Castell and Nie, p. 618. The Attenuation of Cosmic Rays in their Passage through Different Materials.—Steinke and Tielsch, p. 618. Production of Secondaries by Cosmic Rays.—Street, p. 500. Concerning the Production of Groups of Secondaries by the Cosmic Radiation —Street and Johnson, p. 618.

- Conterning the Production of Groups of Secondaries by the Cosmic Radiation.—Street and Johnson, p. 618.
 A Mechanism of Acquirement of Cosmic-Ray Energies by Elec-trons.—Swann, pp. 152, 268 and 399.
 On the Nature of the Primary Cosmic Radiation.—Swann, p. 499.
 Detection of the Ionisation by Individual Cosmic Rays.—Swann, 500.
- p. 500.
- Space Density of Cosmic-Ray Particles.—Swann, p. 618. On the Nature of the Primary Cosmic Radiation.—Swann, p. 618. Cosmic-Ray Nuclear Disintegrations.—Swann and Montgomery,
- or the Limits of Application of the Mathematical Theories of the Vertical Counter Effect in Cosmic Radiation and of the Cosmic-
- Ray Coincidences.—Tuwim, p. 95. General Mathematical Theory of the Vertical Tube Counter Effect of the Cosmic Radiation.—Tuwim, p. 152. Mathematical Theory of the Average Action of the Cosmic Radiation on Detecting Instruments, Shielded or Non-Shielded.—Tuwim, p. 323. First Results obtained in a New Cosmic-Ray Observatory.-Tuwim,
- First Results obtained in the intermination of the Natural Angular p. 388.
 A New Method of Direct Determination of the Natural Angular Distribution of Cosmic Rays [Rotatable System of Tube Counters of Varying Lengths].—Tuwin, p. 499.
- Measurements of Cosmic Rays with a New Type of Counter Tube [and the Action of the Rays on Chemical Elements: Ionisation (Extranuclear Electrons) and Absorption (Nuclei)].—Tuwim, p. 500.
- P. 500. The Interpretation of the Azimuthal Effect of Cosmic Radiation.— Vallarta, p. 562. Passage of Swift Corpuscular [Cosmic] Radiation through a Ferro-Magnetic Substance.—von Weizsäcker, p. 618. Induce of the Earth's Magnetic Field on Cosmic Radiation.—

- Zanstra, p. 617. How Far Do Cosmic Rays Travel ?—Zwicky, p. 209. Cosmic Rays: see also Analysis, Biological, Electrons, Emanation, Geiger, Ionisation, Night Sky, Penetrating, Relations. Cosmic-Ray Observations and Jansky's "Static Hiss" quoted as Evidence of Absolute Cosmic Motion in Ether-Drift Theory.— Miller, p. 617 Miller, p. 617.

- Miller, p. 617.
 A Recording Frequency Counter depending on the Time Constant of a Circuit [Counter for Atmospherics, Tachometer, etc.].— Lugeon and Gurtzman, pp. 457-458.
 Summation Methods in Smoothing Curves.—Vercelli, p. 389.
 Spark Discharge in the Air, Part III.—Asami, p. 499.
 Theory of Spark Discharge in Air [Contradiction of Townsend's Theory : Ionisation due to Electron Impact only: Importance of Rôle of Positue Ion as Space Charge].—Kumagai, p. 151.
 Development of Electric Discharge as affected by the Residual Charge : Study with a Resonant Wave, Continued.—Mochizuki and Kano, p. 151.
 An Experimental Study of Electrical Discharge in Gases at Normal Temperatures and Pressures.—Stephenson, p. 151.
- Temperatures and Pressures.—Stephenson, p. 151. Study of the Electric Discharge [Velocity and Properties of Second Negative Streamer].—Toriyama and Shinohara, p. 499. Bends in the Initial Voltage Characteristic [in Spark Discharges].—
- Toepler, p. 151. Divining of Water, etc. : see Lightning. Hypothesis on the Source of Electrostatic and Magnetic Fields of the

- Hypothesis on the Source of Electrostatic and Magnetic Fields of the Earth.—Machihara, p. 498.
 The Problem of Vertical Earth Currents [and Their Probable Non-Existence].—Gish, p. 617.
 Relation between the Diurnal Variations of the Earth Current and of the Terrestrial Magnetic Field.—Stenquist, p. 208.
 The [Continual] Fluctuations of the Earth's Electric Field [not only due to Local Irregular Disturbances].—Dupérier and Collado, n. 581.
- p. 561. The Influence of Atmospheric Suspensoids upon the Earth's Electric Field as indicated by Observations at Kew Observatory.----Wright, p. 269.
- Wright, p. 209.
 A New Apparatus for the Measurement of the Earth's Magnetic Field.—Bates, p. 267.
 Cosmic Disturbances of the Earth's Magnetic Field and their Influence upon Radio Communication [Comprehensive Survey].
- -Kennelly, p. 267. Sudden Changes in the Earth's Magnetic Field.-Rodés, p. 389.

- The Riddle of the Secular Variation of the Earth's Magnetism [and the Suggestion of a Magnetised Core rotating with a 480-Years' Period].—Schmidt, p. 207. The Eclipse of the Sun of 31st August, 1932, and the "Sounding"

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- Varly].—Guizonnier, p. 151. [Establishment of an Important Relation between] the Electrical Potential Gradient and Atmospheric Pressure.—Guizonnier, p. 561. Motion of Electrons in Heterogeneous Magnetic Fields.—Ertel,
- p. 661. Positive and Negative Electrons Apparently Produced in Pairs [Support to Millikan's Photon Theory of Cosmic Rays].—Langer:
- Anderson, p. 442. On the Paths of Electrons in an Electric and Magnetic Field with
- Axial Symmetry [Theoretical Paper].—Störmer, p. 339. Application of Liouville's Theorem to Electron Orbits in the Earth's Magnetic Field [and Cosmic Ray Intensities].—Swann : Lemaitre and Vallarta, p. 617.
- and Valiarta, p. 617. Electronic Bombardment as a Factor in Atmospheric Phenomena [Blue Colour of Sky, Unpolarised Light from Night Sky Clouds, etc.].—Cohn, pp. 389 and 442. A New Method of Determining the Emanation Content of the Atmosphere and its Application to the Investigation of the Connections with Meteorological Factors and of the Influence of the Emanation Content of the Atmosphere on Measurements of Cosmic Radiation.—Messerschmidt, p. 388. Contribution to the Study of the Fulminant Matter.—Mathias,

- Efficiency of the Geiger-Müller Counter.—Rossi, p. 95.
 Efficiency of the Geiger-Müller Counter and its Connection with Properties of the Normal Glow Discharge.—
- Schulze, p. 95. A Circuit for Recording Multiply-Coincident Discharges of Geiger-Müller Counters.—Johnson and Street, p. 388. Temperature Effect and Its Elimination in Geiger-Müller Tube Counters.—Curtis, p. 268. Associated Problems of Hydrology and Terrestrial Electricity.—

- Associated Problems of Hydrology and Terrestrial Electricity.— Gish, p. 617.
 Non-Existence of Ion Mobility Spectrum in Air.—Varney, p. 151.
 Study of the Methods of Ion Counting [in Air].—Graziadei, p. 210.
 Variations in the Small-Ion Content of the Atmosphere, and Their Causes.—Wait, p. 561.
 On the Jonic Spectrum of the Atmosphere [Summarising Report].— Kähler, p. 32.
 Ionisation Charts of the Upper Atmosphere [from Chapman's Theory].—Millington, p. 32.
 The Value of the Townsend Coefficient for Ionisation by Collision at Large Plate Distances and Near Atmospheric Pressure.—

- at Large Plate Distances and Near Atmospheric Pressure.

- at Large Plate Distances and Near Atmospheric Pressure.— Sanders, p. 93. The Ionisation due to Gamma and Cosmic Rays in Oxygen and Xenon [Preliminary Communication].—Masuch, p. 95. Electronic Ionisation at Low and High Pressures [in Nitrogen, Oxygen and Air].—Masch, p. 151. Some Comments on the Relation between Ionisation and Ionisation Current in Gases at High Pressures.—Harper, p. 210. On the Formation of Negative Ions according to Quantum Mech-anics [and the Light of the Night Sky].—Rocard, p. 98. Relations between the Combination Coefficients of Atmospheric Ions.—Whipple n. 498.
- Relations between the Combination Coemclents of Atmospheric Ions.—Whipple, p. 498. Slow-moving Ions in the Atmosphere.—Wait and Torreson, p. 269. An Improvement to the Kyldonograph.—Hartje, p. 33. An Improvement to the Kyldonograph : Correspondence.— Müller-Hillebrand : Hartje, p. 151. Investigation of the Action of the Kyldonograph.—Wilkinson, ~ 400

- Investigation of the Action of the Kyldonograph.—Wilkinson, p. 499. A New Wide-Angle Lens [applicable to Photography of Lightning Flashes, Aurora, etc.].—Schulz, p. 33. A Lens for Cosmic-Ray Electrons.—Swann and Danforth, p. 500. Lichtenberg Figures in Gases and Liquids.—Toriyama, p. 389. Lightning and Its Behaviour to Overhead Lines.—Aigner, p. 93. Influence of Geophysical Factors on the Frequency of Lightning Strokes on an Area.—Bogoiavlensky, p. 561. A Destructive Lightning ; a New Stereoscope.—Boys, p. 389. Influence of the Geological Composition of the Ground on the Ionisation of the Air and on the Incidence of Lightning.— Daużere, p. 441.
- Daużere, p. 441. Daużere, p. 441. Effect of Lightning on Transmission Lines [Steepness of Wave Front can reach 15 to 20 Thousand kv/Microsec. : Highest Potential 5 Million Volts : etc.].—Fortescue, p. 389. The Surge-Crest Ammeter [for Lightning Study].—Foust and
- Kuehni, p. 151. On the Propagation of a Lightning Discharge through the Atmo-sphere.—Halliday, p. 208.

Atmospherics and Atmospheric Electricity.

- A Method of Protection against Direct Lightning Strokes [for Points on an Overhead Line particularly liable to such Strokes] -Holzer, p. 93.
- On the Velocity of the Extension of a Lightning Flash .-- Jehle, p. 441.
- Ball Lightning.—Jones, p. 33. Experimental Studies on the Propagation of Lightning Surges on the 154 kv Tokyo Line of the Nippon Electric Power Company .-Kasai, p. 268. The Causes of the Prevalence of Lightning Strokes at Certain Points
- The causes of the Prevalence of Lighting Stocks at Certain Points on a High-Tension Line [Effect of Subterranean Water : Hazel-Twig Divining].—Lehmann, p. 93.
 Lightning Study aided by a New Instrument [the Surge-Crest Ammeter].—Lewis, p. 151.
 Some Points concerning Lightning Conductors [including Calculation of Probable P.Ds between the Conductor Tip and Earth].—

- tion of Probable P.Ds between the Conductor Tip and Earth].— Monney, p. 617.
 On the Causes of the Predilection of Lightning for Certain Points on High Tension Lines.—Müller-Hillebrand and others · Lehmann, p. 151.
 Overhead Lines and Lightning Disturbances according to Recent Foreign Publications.—Müller-Hillebrand, p. 93.
 Attempt at a Theory of the Lightning Flash.—Ollendorff, p. 441.
 Lightning [Height of Cloud and Extent of Charge deduced from Form of Wave Front: Duration and Nature of Discharge from Rear Stope : etc. 1—Reak p. 399.
- Form of Wave Front: Duration and Nature of Discharge from Rear Slope: etc.].—Peek, p. 389.
 Lightning Research. American and Continental Observations— Influence of Radio-Activity in the Soil—Explanation of "Dows-ing" [Summary of Papers at the International Electrical Con-gress].—Peek, Fortescue, Dauzère, Bogoïavlensky and Chatelain, Rudenberg, and others: Lehmann, p. 32.
 Gaseous Breakdown at Normal Pressure [Application to Growth of Lightning Flash].—Sämmer, p. 616.
 Development of the Lightning Discharge.—Schonland and Collens, p. 616.
- p. 616.
- Special Meeting of the Union of Electricity Works in Saxony, for Discussion of Lightning Problems.—Toepler and others, p. 151. Protection against Lightning by the "Distant Conductor."—Walter.
- p. 441.
- Protection against Lightning by the "Distant Lightning Conductor" [and the Calculation of the Area protected by a Vertical Well-Earthed Rod of given Height].—Walter, p. 268.
- Earthed Rod of given Height].—Walter, p. 268. The Apparent Effect of Magnetic Activity upon the Secular Variation of the Earth's Magnetic Field.—McNish, p. 617. Variation of the Horizontal Component around Days of Magnetic Calm.—Eblé, p. 442. Contribution to the Study of Magnetic Disturbances.—Lévine,
- p. 267. Secular Changes of the Magnetic Elements, Ottawa, 1500-1930.-
- Herbert, p. 561. On the Influence of a Superposed Magnetic Field on the Dielectric Behaviour of Some Solid, Liquid and Gaseous Bodies.—Schmid,
- p. 33. Field Energy of Magnetic Storms.—Chapman, p. 389. Some Problems of Modern Meterorology, No. 10. Terrestrial Magnetism—the Magnetic Variations of Short Duration.—Goldie, p. 389.

- p. 389.
 Physics in Meteorology.—Simpson, p. 32.
 Méteors and the 80-90 km Layer of the Earth's Atmosphere.— Malzev, p. 561.
 Meteors: see also under "Propagation of Waves."
 New Observations on the Spectrum of the Night Sky [and a Comparison with the Auroral Spectrum].—Dufay, p. 617.
 Spectra of the Night Sky, the Zodiacal Light, the Aurora, and the Cosmic Radiations of the Sky.—Silpher, p. 617.
 Some Photographs of the Tracks of Penetrating Radiation [showing Positive Electrons].—Blackett and Occhialini, p. 343.
 Penetrating Radiation from ThunderCouds.—Cairns, p. 561.
 Thunderstorms and Penetrating Corpuscular Radiation at Sea-Level.—Rossi, p. 499.

- Level.—Rossi, p. 499. On the Nuclear Disintegration produced by the Penetrating Radia-
- tion.-Rossi, p. 562.
- Secondary Effects of Penetrating Corpuscular Radiation : Anomalies of Absorption of Penetrating Radiation --- Rossi : Rossi and

- of Absorption of Penetrating Radiation.—Rossi. Toosi -Crino, p. 95. Evidence of a Penetrating Radiation from Thunderstorms.—Schon-land and Viljoen, p. 33. On a Penetrating Radiation from Thunderclouds.—Schonland and Viljoen, p. 442. The Distribution of the Ionising Particles of the Penetrating Radia-tion in Relation to the Magnetic Meridian.—Viljoen and Schon-land n. 549. land, p. 562.
- Maid, p. 302.
 Spectrum and Latitude Variation of Penetrating Radiation.— Williams, p. 388.
 Some Common Periodicities in Radio Transmission-Phenomena.— Kenrick and Pickard, p. 265.
 Progress-Report of the International Polar Year of 1932-33.—
- Fleming, p. 617. Ionic Over-Voltage Protectors.—AEG, p. 389. Electric Charges on Rain Drops.—Banerji and Lele, p. 151.

- A Note on an Automatic Field Strength and Static Recorder.-Mutch, pp. 222-223.
- Relations among Fluctuations of the Cosmic-Ray Ionisation, of the Terrestrial Magnetic Field, of the Atmospheric Potential Gradient and of the Absolute Humidity.—Broxon, Merideth and Strait,

- and of the Absolute Humidity.—Broxon, Merideth and Strait, p. 617. On the "Return" Shock.—Mathias, p. 94. A Noticeable Period of Solar Activity—the First Fortnight in February.—Memery : Esclangon, p. 267. The Researches on the Relations between Solar and Terrestrial Phenomena.—Abetti, p. 389. The Time Interval between Solar Phenomena and Terrestrial Magnetic Disturbances.—Maurain, p. 441. The Space Charge in Relation to the Chemical Components of the Atmosphere.—Stoppel, p. 32. On the Development of the Space Charge of a Spark Gap with an Impulsive Voltage.—Sämmer, p. 282. Density of Electronic Space Charges of Störmer's Aurora Theory Insufficient to Cause Long-Delay Echoes.—Dostal : Störmer, p. 33. p. 33. The Behaviour of Glass-Enclosed Single Spark-Gaps to Surges
- [and the Advantage of Radioactively Produced Ionisation].— Berger, p. 617. The Internal Stability of Masses of Air of Various Origins.—Fontell,
- p. 150.
- p. 100. Theory of Elastic Systems Vibrating under Transient Impulse, with an Application to Earthquake-Proof Buildings [and to the Effect of Static on Radio Circuits].—Biot, p. 269. Electrical Disturbances ["Static Hiss"] of Extraterrestrial Origin.

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- on Day of Large Sunspot : Apparent Height about 300 Miles] p. 323.
- p. 023. Sunspots: see also under "Propagation of Waves." The Recording of Surges [Two Simple Equipments as Substitutes for the Cathode-Ray Oscillograph].—Dodds and Fucks, pp. 635-636.

- b30.
 The Electric Field of Overhead Thunderclouds.—Banerji, p. 32.
 The Polarity of Thunderclouds.—Halliday, p. 32.
 Summer Thunderstorms.—Bower, p. 323.
 Formation of Local Thunderstorms. Part II. Processes in the Free Atmosphere above Lindenberg on 2nd and 3rd July, 1932. von Ficker, p. 389. The Influence of Thunderstorms on Radio Propagation.—Fuchs,

- Inc influence of Thunderstorms on Kadlo Propagation.—Puchs, p. 442.
 Work of United States Hydrographic Office in Terrestrial Magnetism and Electricity [Locating Thunderstorms by Cathode-Ray Direction Finders].—Gherardi, p. 267.
 Precaution against Disturbances caused by Thunderstorms on Electric Power Transmission Lines [Thunderstorm Observations and Warnings in Tokyo and Yokohama].—Takasawa, p. 498.

- A Census of Summer Thunderstorms, p. 32. Thunderstorms : see also Penetrating. The Ultra-Violet Transmission Coefficient of the Earth's Atmosphere. —Rockwood and Sawyer, p. 32.
- Measurements of Ultra-Violet Solar Radiation in Various Localities [at Various Heights at Various Stations in Europe, North Sea and Atlantic Ocean].—Coblentz, Stair and Hogue, p. 151.

PROPERTIES OF CIRCUITS

- PROPERTIES OF CIRCUITS New Types of Thermionic Amplifier [particularly the Use of Virtual Negative Resistance in "Compensated" Resistance-Coupled Amplifiers].—Denina, p. 97. High-Frequency Amplifier with Series Resonant Circuit [as Plate Load instead of Usual Parallel Resonant Circuit : Improved Results in Amplification and Stability, e.g. in I.F. Amplifier of Superheterodyne Receiver].—Iso, p. 500. Note on Tuned-Anode and Transformer-Coupled R.F. Amplifiers.— Marinue n. 303.
- Marique, p. 393.

- Marique, p. 393. The Balancing and Stabilising of H.F. Amplifiers.—Ure, Grainger and Cantelo, p. 500. The A.C. Resistance of Straight Wires of Circular Section composed of Several Concentric Layers [e.g., Tinned or Oxidised Copper Wire].—Ekelöf, p. 323. Relations between the Parameters of Coupled-Circuit Theory and Transducer Theory, with Some Applications [Determination of Conditions for Resonance in a Chain of Coupled Circuits].— Brainerd, p. 324.
- Brainerd, p. 324. The Resonance Frequencies of Two Coupled Oscillatory Circuit [and a New Method of Frequency Analysis].—Fehr and Kreielsheimer, p. 562. The Direct Solution of **Coupled** Tuned Circuits.—Kelley, p. 98.

Properties of Circuits.

- Contribution to the Study of the Stability of Oscillations in **Coupled** Circuits [e.g. in Oscillating Circuit coupled to Wavemeter].— Mercier, p. 443. Frequency of Oscillations in Two Inductively **Coupled** Circuits [One being in a Valve Anode Circuit : the Theoretical Existence of Three Frequencies].—Rousseau, p. 562.

- Three Frequencies].—Rousseau, p. 562. Transformer Coupling Circuits for High-Frequency Amplifiers.— Christopher, p. 34. Youpled Circuits : see also Lecher Wire. Coupling and Coupling Coefficients.—G.W.O.H., p. 35. The Experimental Demonstration of the Effects of Coupling of Harmonic Motions, as illustrating Phenomena in Quantum Mechanics [Study of Coupled Electrical Circuits].—Burton, p. 98. A New Method of Radioplectric Coupling. The "Diffusion"
- A New Method of Radioelectric Coupling : The "Diffusion" Coupling.—Cordebas, p. 622. Crosstalk as a Reflection Phenomenon.—Ohashi, pp. 35 and 153. Potentials, Resistances and Tuning in Damped and Undamped Circuits : Errata.—Osnos, p. 97.
- The Action of Damping Reduction [by Retroaction] in Broadcast Receivers.—Kautter, pp. 622-623. Decoupling Efficiency [and a Convenient Alignment Chart].—Bar-
- Decouping Emciency [and a Convenient Alignment Chart].—Bar-clay, p. 500. The Impedance of Defective Loaded Lines, particularly One with Abnormal Wire-to-Wire Capacity in a Loading Coil Section.— Adams and Haas, p. 394. "Demodulation " [and in particular the "Detector Choking Effect"].—Lewis: Colebrook, p. 96. Some Notes on Demodulation.—Roder, pp. 212-213. The Efficiency of Valve Detection.—Kahan and Dierewianko, p. 96

- p. 96. The Detection of Modulated Oscillations [and the Deficiencies of the
- The Detection of Modulated Oscillations (and the Deficiencies of the Usual Valves for Both Methods of Detection).--Varret, p. 96. Theory of the Detection of Two Modulated Waves by a Linear Rectifier.--Aiken, p. 392. Diode Detection Analysis.--Kilgour and Glessner, p. 566. Voltage Amplification with High Selectivity by means of the Dynatron Circuit.---Colebrook, p. 212. Dynatron : see also Frequency. Equivalent Circuits [and Their Methods of Use].--Starr, p. 35. Replacement of a Mechanical Vibrating System by an Equivalent Electrical Circuit.--Domerque, p. 35. The Empirelent Circuit of a System of Two Inductively Coupled

- The Equivalent Circuit of a System of Two Inductively Coupled Circuits.—Rimin, p. 35. Two-Element Band-Pass Filters [and the Use of Charts].—Beatty,
- p. 98. On the Theory of Electrical Filters.--Bubenik, p. 97.

- On the Inforty of Electrical Filters,—Budenik, p. 97. Resistance in Band-Pass Filters,—Buffery, p. 35. Critical Reviews of Books and Papers on Electric Filter Circuits.— David: Cauer: Guillemin: Jaumann: Strutt: Beatty, p. 443. The Theory of Band-Pass Filters for Radio Receivers.—Oatley, p. 98.
- Method of Calculating the Attenuation in a Band-Pass Filter arbitrarily composed of Inductances, Resistances, Capacities, Transformers.—Pleijel, p. 500. The Working Attenuation of the Simplest Filter Chains.—Tcha-
- janow, p. 153.
- janow, p. 153. The Behaviour of Wave-Filters when Loaded with Saturated Iron Chokes.—Wassmann, p. 97. Filters: see also Coupled, Coupling, Multipole, Network, Trans-former : and under "Reception," "Acoustics," and "Subsidiary
- former : and under "Reception," "Acoustics," and "Subsidiary Apparatus." Fly-Wheel and Series Circuits with Self-Excited Oscillations pro-duced by Thermionic Valves.—Heegner, p. 154. A Fourier Analysis of Radio-Frequency Power Amplifier Wave Forms.—Hallman, p. 37. A Simplified Frequency-Dividing Circuit [using One Pentode Valve].—Andrew, p. 578. Frequency Division by means of a Dynatron Oscillator.—Kahan, p. 97.
- p. 97.
- Frequency Doubling in a Triode Vacuum Tube Circuit .- Smith, p. 210.
- Investigations on the Setting-In Point of Grid Current in Amplifier Valves.-Rothe, p. 95.
- Grid Current Compensation in Power Amplifiers.—Baggally, pp. 217-218.
- Extension of the Methods of Heaviside's Calculus in Calculation of Circuits containing Parameters varying with Time.-Neufeld, p. 153.
- Mutual Impedance of Long Grounded Wires when the Conductivity of the Earth varies Exponentially with Depth.—Gray, p. 327. The Significance of the Sign of a Mutual Inductance.—Nimmo and
- Poole, p. 35. Iterative Impedances [of Dissymmetrical Quadripoles].—Pomey, p. 324.
- p. 524.
 Amplitude Characteristics [Resonance Curves] of Coupled Circuits having Distributed Constants [Bridge-Coupled Lecher Wire Pairs].—King, p. 618.
 The Relation between the Disturbance Current and the Degree of Asymmetry in Lines subject to Induced Noise.—Schotte, p. 443.
 Invariant Properties of the Extreme Fringes of Inducing and Induced [Magnetic] Fields.—Lehmann, p. 98.

- Can Magnetisation Formulae be applied to the Quantitative Treatment of Building-Up Processes in Circuits containing Iron ? -Hak, p. 97.
- Real Power Matching and Apparent Power Matching [for Trans-mission of Maximum Power from Source to Load].—Fischer, pp. 34 and 153.
- 34 and 153.
 An Example of a Complete Analogy between Electrical and Mechanical Oscillation.—Ramsauer, p. 500.
 A New Analogy between Mechanical and Electrical Systems.— Firestone, p. 269.
 Mechanical Models for the Investigation of Electrical Stability Deablers Description 5, 2004.
- Problems.—Darricus, p. 390. Superposition of Two Modulated Radio Frequencies [and the Dis-
- Specification of two involution and the requestions fail the Dis-tortions in the Resulting Envelope].—Roder, p. 210. New Results in the Calculation of Modulation Products [applicable to Linear, Square Law and Other Rectifiers, Peak Choppers, etc.].—

- New Results in the Calculation of monutation rroutics (appricate to Linear, Square Law and Other Rectifiers, Peak Choppers, etc.].— Bennett, p. 389.
 Theory and Application of Symmetrical Multipole Connections.— Baerwald, p. 35.
 The Production of Negative Conductances by means of Retroactive Couplings.—Kautter, p. 447.
 A Dynamic Characteristic of Thermionic Vacuum Tube with Negative Resistance [and the Conditions for the Occurrence of the "Blocking." Phenomenon].—Fukuta, p. 35.
 A Method for Calculating Transmission Properties of Electrical Networks consisting of a Number of Sections [using Difference Equations].—Alford, p. 619.
 Equivalent Circuits of an Active Network.—Brainerd, p. 210.
 Note on Network Theory [General Expressions for Passive "Transducers" or Quadripoles connected in Various Ways to form a Resultant Passive Transducer].—Brainerd, p. 35.
 Note on Bartlett's Bisection Theorem for 4-Terminal Electrical Networks.—Foster, p. 35.
 Geometrical Circuits or Electrical Networks.—Foster, p. 35.
 Geometrical Circuits or Electrical Networks.—Foster, p. 35.
 Kutenson of Maxwell's Rule for Analysing Electrical Networks.—Ku, p. 563.

- Ku, p. 563.
- Transmission Curves of High-Frequency Networks.—Model, p. 210. Initial Phase Angles of Low-Pass Networks, and the Phase Com-pensating Networks of the "Bridged-T" Type.—Nagai, p. 97. On the Electrical Constants of Meshed Networks.—Ravut, p. 153.

- On the Electrical Constants of Meshed Networks.—Ravūt, p. 153. A New Theorem for Active Networks.—Starr, p. 618. Non-Linear Characteristic Curve Families [Application to Triode Amplifier Valves].—Feldtkeller and Jacobi, p. 619. Mathematical Expression of a Saturation Curve : Useful in Cal-culating Non-Linear Circuits.—Summers, p. 390. Non-Linear Circuits Applied to Relays.—Suits, p. 403. A Note on Nonlinearity in Transducers used in Communication [and] Its Correction by a Series Compensating Transducer].— Caporale, p. 563. On the Theory of the Freely Oscillating Circuit.—Rousseau : Osnos. p. 210.
- Osnos, p. 210.
- Osnos, p. 210. New Abnormal Oscillating Phenomena in an Oscillation Circuit including an Externally Excited Saturated Transformer.— Watanabe and Takano, p. 152. Building-Up of a Self-Oscillation in an Oscillation Circuit including a Periodically Varying Inductance [H.F. Alternator of Inductor Type].—Watanabe, Saito, and Kaito, p. 500. The Mechanism of the Production of Oscillations.—Le Corbeiller, a 445.
- p. 445.
- Some Electrical Oscillators of Special Shape [Forks with Prongs of Different Length, with Prongs at Right Angles, etc.].-Lindman,
- D. 270. On the Theory of Oscillatory Condenser Discharges.—Thomson; p. 269.
- Contribution to the Theory of the Natural Frequencies and Self-Excitation in [Coupled] Electrical Oscillatory Circuits.--Kaiser, p. 323.
- p. 323.
 Oscillatory Circuits [Mathematical Investigation of Toroidal Inductance connected to Condenser].—Dacos, p. 563.
 Calculation of Output and Distortion in Symmetrical Output Systems.—Nelson, p. 152.
 Simplification of the Calculation of Parallel-Connected A.C. Resistances [e.g., Equivalent Circuit of Piezoelectric Crystal].—Vilbig, p. 610.
- p. 619.
- A Practical Analysis of Parallel Resonance [with Applications to the Adjustment of Radio Apparatus].—Lee, p. 269. Discussion on "A Practical Analysis of Parallel Resonance."— Seeley: Lee, p. 500. Further Note upon the Pentode with Capacitive Coupling.—Sims, p. 182
- p. 153.
- Equivalent Circuit of a Blocking-Layer Photocell.---Wood, p. 324. Sustained Oscillations [from a Photoelectric Cell Circuit].--Hochard,
- p. 391.
- p. 391.
 Pulse Factor and Pulse Damping.—Führer, p. 98.
 The Quadripole Properties of the Two-Wire Two-Valve Repeater and Their Dependence on Its Internal Construction.—Byk, p. 613.
 Law of Reciprocity for Changes involving the Removal of One Degree of Freedom in Linear Systems.—Bloch, p. 443.
 Discussion on "Some Notes on Grid Circuit and Diode Rectification."—Kelly : Nelson : Terman, pp. 392-393.

Properties of Circuits.

- Mechanical Relaxation Oscillations [Application of Electrical Theory
- Mechanical Relaxation Oscillations [Application of Electrical Theory to Mechanical Systems: Experimental Confirmation].—Kajdanovsky and Chaikin, p. 619.
 The Damped Resonance Circuit with Iron-Cored Inductance [Graphical Determination of Stationary Conditions].—Diesendort, p. 500.
 The Representation of [Single-Peak] Resonance Curves by "Selectivity Indexes."—Kafka, pp. 448-449.
 Some Experiments on the Retardation Networks [the Adjustment of the Delay Time, and the Action of Transients].—Nagai, p. 97.
 A Retroaction Coupling Independent of Frequency, for Valve Oscillators and Oscillating Audions [derived from the Loftin White Circuit].—Below, p. 96.
 Circuits with a Capacity in Parallel with a Saturated Diode.—Dei, p. 390.

- 390
- p. 390.
 A Skin-Effect Phenomenon [in Concentric Pipe Feeders : Resistance of a Hollow Cylindrical Conductor may Increase if its Thickness is Increased, for Very High Frequencies].—Schelkunoff, p. 153.
 Skin Effect in a Stratified Cylinder of Circular Section.—Strutt,
- p. 269.

- p. 269.
 The Magnetic Field of a Solenoid Oscillating at Radio Frequencies. —Stuhlman and Githens, p. 35.
 Sub-Harmonics in Forced Oscillations in Dissipative Systems.— Pedersen, pp. 626-627.
 Some General Resonance Relations and a Discussion of Thevenin's [Pollard's] Theorem.—Brainerd, p. 563.
 [Air Cored] Transformers with Variable Coupling.—Siegel, p. 443.
 Ideal Transformer, Ideal Synapter [dealing also with Phase] and Perfect Transducer.—P. C. Vandewiele, p. 443.
 Theory of Elastic Systems Vibrating under Transient Impulse, with an Application to Earthquake.Proof Buildings [and to the Effect oi Static on Radio Circuits].—Biot, p. 269.
 Transient Régimes [in Viscous Liquids].—Crausse and Baubiac, p. 289.
- p. 269.

p. 209. Transients in Negative Constant Series Circuits.—Verman, p. 500, A Study of Transitory Régimes and Time Constants for the Prin-cipal Circuits used in Wireless Engineering.—Rocard, p. 97.

TRANSMISSION

New Radio Telephone Equipment for Transport Airplanes; and A Three-Frequency Radio Telephone Transmitter for Airplanes. —Martin: Tinus, p. 502.

Airport Radio Transmitter [Western Electric Type 10A] .--- Knott,

- p. 99. Determination of Grid Driving Power in Radio-Frequency Power
- Amplifiers.—Thomas, p. 621. The Balancing and Stabilising of High-Frequency Amplifiers with Special Reference to Power Amplifiers for Radio Transmitters [for Naval Ship Use].—Ure, Grainger and Cantelo, pp. 446 and 502
- For Navar Sin Usel.—Ofe, Granger and Cantedo, pp. 440 and 502.
 Experimental Examination of the Theory of the Barkhausen Oscillations [Möller, 's "Sorting-Out" Theory of the Electrons].— Helmholz: Möller, p. 390.
 Calculation of the Mechanism of Oscillation Onset with a Valve in the Barkhausen-Kurz Oscillations.—Orgel, p. 270. Investigation of Barkhausen-Kurz Oscillations.—Orgel, p. 270. Investigation of Barkhausen-Kurz Oscillations.—Alfvén, p. 619.
 Electronic 'Phone Break-in : Another 'Phone Break-In System.— Mesa: Ashlock, p. 99.
 Break-In Operation with Crystal Control : Blocked-Grid Keying applied to a High-Power Transmitter.—Foreman, p. 155.
 A Low-Power Broadcast Transmitter (100 Watts Output Basic Unit, extensible up to 1000 Watts by adding Amplifier Unit).—Kishpaugh, p. 37.
 New High-Power [Broadcast] Transmitter to replace Daventry Long-Wave Set [using "Series Modulation"].—pp. 211 and 271.

- 271. Low Power Radio Transmitters for Broadcasting.-Kishpaugh
- and Coram : Western Electric Company, p. 271. Carrier Noise in Short-Wave Transmitters.—Gracie and Dixon, p. 211.
- Line-Controlled Synchronisation of Common-Wave Transmitters. -Runge, pp. 285-286.
- The Question of the Choice of Common-Wave Systems [Synchron-ised or Unsynchronised].—Gerth, p. 391. Time Delay Effects in Synchronous [Common-Wave] Broadcasting.
- -Aiken, pp. 460-461. Device for Preventing Breakdown of Neutralising Condenser in

- Device for "Preventing Breakdown of Neutralising Condenser in High-Power Amplifiers.—Churchill, p. 155.
 More on Transmission-Line [" Impedance-Line "] Interstage Coupling [between Exciter and Power Amplifier], p. 502.
 Crystal-Controlled Transmitter with Variable Wavelength.—Tele-funken Company, p. 271.
 The Crystal Drive of the Experimental Short-Wave Broadcasting Station G5SW.—Parkin, p. 565.
 A More Stable Crystal Oscillator of High Harmonic Output [Screen-Grid Valve with Tuned Circuit between Cathode and Earth, Crystal between Grid and Cathode].—Lamb, p. 502.
 Where does a Decaying Oscillating Process end, and a Building-Up Process begin?—Barkhausen and Hässler, p. 619.
 Decimetre Waves : see under Ultra-Short.

- The Dynatron Oscillator [and the Suitability of the Mazda AC/S2 Valve for Frequencies up to at least 60 Megacycles/Sec. with Normal Dynatron System].—Scroggie: Colebrook, p. 99. Crystal Control applied to the Dynatron Oscillator.—MacKinnon,
- p. 155.

- p. 155.
 Theoretical and Experimental Studies on the Frequency Stabilisation of the Dynatron-Type Oscillator [including the Use of an Additional Inductance in the Dynode Circuit].—Hayasi, p. 502.
 The Inner-Grid Dynatron and the Duo-Dynatron [Single Tetrode Beat-Frequency Oscillator].—Hayasi, p. 620.
 Effect of Circuit Parameters on the Constancy of the Frequency of a Pilo-dynatron.—Mears, p. 620.
 The Effect of the Curvature of the Characteristic on the Frequency of the Dynatron Generator (Frequency Changes greater than can be accounted for by Curvature alone).—Moullin, p. 664.
 The Inter-Electrode Capacitance of the Dynatron with Special Reference to the Frequency Stability of the Dynatron Generator.—Baker, p. 565.

- Reference to the Frequency Stability of the Dynatron Generator. --Baker, p. 565. Maximum Efficiency from the Type 52 Valve: 800 Watts in Aerial with 1 Kilowatt Input.--Perrine, p. 37. Efficiency in the Output Amplifier [and Aerial]: Some Suggested Methods of Increasing Antenna Power.--Schnell, p. 99. Electronic: see under Ultra-short. A Graphical Method for Determining the Transit Times of Electrons in a Three-Electrode Valve under Conditions of Space-Charge Limitation.--McPerrice. p. 564.
- Limitation.—McPetrie, p. 564. The Determination of the Interelectrode Times of Transit of Electrons in Triode Valves with Positive Grid Potentials.—
- Electrons in Triode Valves with Positive Grid Potentials.—
 McPetrie, p. 620.
 Electron-Coupled Oscillators for the Small Transmitter [giving Steady-Frequency Note characteristic of Crystal Control, with the possibility of Changing the Frequency].—Grammer, p. 37.
 Power Type Electron-Coupled Exciter Unit [and the Measurement of Dower by Lecendence the area and Photemen in Coll.
- of Power by Incandescent Lamp and Photronic Cell] -Houldson, p. 325.
- p. 325.
 Diminution of Fading by Alternating the Transmitted Wave between Two Neighbouring Wavelengths.—USSR Electrot. Association, p. 271.
 Elimination of Fading Compensating Devices by Choice of Modu-lation Curve of Transmitter, and Rectifying Curve of Receiver, as Identical Exponential Functions.—Roosenstein, p. 446.
 A Radio Transmitter for the Itinerant Flyer.—Bishop: Bell Laboratories. p. 155.

- A Radio Transmitter for the finite and rate and the source of the source 391.
- The Modulated C.W. Transmitters of the French Coast Stations .--

- The Modulated C.W. Transmitters of the French Coast Stations.— Bruniaux, p. 211.
 Frequency Multiplication by Superposition of Two Oscillations each modulated at the Oscillating Frequency, One in Phase and the Other in Opposed Phase.—Wassermann, p. 445.
 The Required Minimum Frequency Separation between Carrier Waves of Broadcast Stations.—Eckersley, p. 285.
 Frequency Stabilisation by Coupling the Grids of Push-Pull Circuit through a Quartz Crystal.—Elektroswias, Leningrad, p. 271.
 Limits of Frequency Stability of Modern Short Wave Transmitters.— Vallauri, p. 155.
 An Oscillator having a Linear Operating Characteristic [and High Frequency Stability].—Arguinbau, p. 211.
 Study on the Frequency Variation of Valve Generators.—V. Further Comparison of Frequency Variation of Stabilisation using Low Excitation.—Ishikawa, p. 37.
 The Interdependence of Frequency Variation and Harmonic Con-tent, and the Problem of Constant-Frequency Oscillators.— Groszkowski, pp. 390 and 564.
 Frequency Variation, Stability: see also Dynatron, Electron, Stabilisation
- Frequency Variation, Stability : Stabilisation. see also Dynatron, Electron,
- Researches on the Establishment of a Limit of Intensity for the Harmonics of Transmitting Stations.—Krulisz and Wolski, p. 391.
- Suppression of Transmitter Harmonies.—Dietsch, p. 565. Tunable Hum [from Gas and Vapour Rectifiers] : Its Cause, Effect and Elimination.—Dellenbaugh, p. 155. Modulated Light-Ray from Airship as a Link in Broadcast Trans-
- Magnetoelectric Radiations from Ring-Shaped or Spiral Oscillators.
 --Lindman, p. 445.
- The H.F. Currents produced by H.T. Magnetos.—Jaffray, p. 271. A Note on the Theory of the Magnetron Oscillator [Correction to Okabe's Constant by allowing for Cardioid Path of Electron].— Hoag, p. 620. On the Generation of the Medium-Wave Oscillation by the Split-

- On the Generation of the Medium-wave Oscillation by the Split-Anode Magnetron.-Morita, p. 620. Magnetostatic and Magnetron: see also under Ultra-short. A System of Double Modulation for Duplex Radio Communication on Micro-Waves.-Carrara, p. 54. The Indirectly Heated Triode as Generator of Micro-Waves.--Giacomini, p. 501.

Transmission.

- The Generation of Micro-Waves with Special Valves in a Retarding-Field Connection.—Gossel: Kohl, p. 564. Modulating the Screen-Grid R.F. Amplifier: How It Behaves with Grid, Screen-Grid and Plate Modulation.—Robinson, p. 155. Modulation and Distortion Measurements by means of the Cathode-Daw Generation Screen Grad Egent a. 00
- Ray Oscilloscope.—Bagno and Egert, p. 99. Frequency Modulation and the Effects of a Periodic Capacity Variation in a Non-Dissipative Oscillatory Circuit.—Barrow, p. 565.
- Getting Quality Performance with Class B Modulation : Practical Design and Operating Data for Best Tube Combinations.—Collins, p. 446
- Series Modulation [and Its Advantages over Other Systems] .-
- A Note on Grid-Bias Modulation [Necessity for Capacity of Class B Amplifier equal to Ten Times the Carrier Power].—Hallman, p. 155.
- Making Practical Use of Grid-Bias Modulation : Applying It to Amateur 'Phone Transmitters.—Isberg, p. 37. Modulation by Two-Grid Valves.—Lorenz Company: RCA., p.
- 271 Band Widths in Frequency- and Amplitude- Modulation .- Lüschen,
- p. 99. Increase of Modulation in Radiotelephonic Transmitters .- Marietti,
- p. 502.
 Note on an Impulse Indicator [for Monitoring Modulation of Wireless Transmitters and Sound Films].—Rocard, p. 621.
 The Graphical Treatment of Modulation Problems [including Applications to the Transmission of Carrier and Side-Bands from Separate Aerials, and to Common-Wave Broadcasting].—Roder, AMB
- p. 446. A New Method of Obtaining Frequency Modulation [by Varying Resistance through Use of R. F. Transmission Line].—Scott:
- Resistance through Use of K. F. Fransmission Line,—Scott: Eastman, p. 565. New Developments in the Design of Broadcasting Transmitter [Chireix De-phasing Modulation, at "Radio-Paris" and "Poste Parisien "].—Singer, p. 99. Circuit for Modulation by Grid Direct Current.—Telefunken Com-pany: Buschbeck, p. 271. Modulation Products in a Power Law Modulator.—Tynan, p. 621.
- Modulation : see also Multiple. Class B Audio Amplifier as a Modulator for Broadcasting Stations.
- Barton, p. 621. Application of Transformer-Coupled Modulators [and the Higher Efficiency and Decreased Distortion of Class B Amplification].— Hutcheson, p. 565. A Simplified Method of Modulator Design.
- -Laport, p. 621
- Elementary Theory of a System of Multiple Modulation of a R.F. Oscillation [a Method of Obtaining Maximum Efficiency with Linear Modulation up to the Highest Modulation Percentage] —
- Fayard, p. 621. perating Mechanisms of Negative Resistance Oscillators (IV): Inspections on the Auxiliary Equation of Oscillation.—Usui, Operating
- p. 155. Special Kinds of Neon Tube Oscillations [using Cylinder and Co-axial Wire Electrodes and a Magnetic Field].—Okabe, p. 99. Non-Linear : see Relaxation.: also under "Properties of Cir-
- cuits.
- On the Spontaneous Generation of Oscillation in Low Pressure

- On the Spontaneous Generation of Oscillation in Low Pressure Discharges.—Mitra and Syam, p. 36.
 The Mechanism of the Production of Oscillations [General Mathe-matical Treatment].—le Corbeiller, pp. 36 and 445.
 Different Forms of Oscillation obtainable with Thermionic Valves.— Vecchiacchi, p. 620.
 Circuits within Circuits : a Discussion of Parasitic Oscillations in Neutralised Amplifiers.—Grammer, p. 502.
 Stringent Test for Photoelectric Cell [Half-Mile Optical Link in Broadcast Transmission], p. 271.
 Sustained Oscillations [from a Photoelectric Cell Circuit].—Hochard, p. 391.
- p. 391.

- P. 651. Pliodynatron : see Dynatron. The Generation of Polyphase Oscillations with the aid of Dynatron Circuits.—Groszkowski, p. 445. Duplex Portables [Portable Self-Contained "Transceivers" for Transmission and Reception, weighing 23 Pounds].—Keefer and Correct = 569. Grant, p. 502.
- Grant, p. 502. Power Ratios in High Power Radio Transmitters [Values for All Stages represented on Single Logarithmic Diagram: Deter-mination of Efficiencies].—Steudel, p. 37. Generation of Current with Rectangular Wave-Form by Glow-Discharge Tubes or Dynatrons.—Telefunken, p. 621. On Self-Excited Non-Linear Valve Oscillations [Relaxation Oscil-lations & Evenemental and Theoretical International Con-
- lations : Experimental and Theoretical Investigation] .-- Straub, p. 620.
- p. 620. Resonance in Three-Electrode Valves.—Gill and Donaldson, p. 444. Screen-Grid Valves in Quartz-Controlled Transmitters [for Short and Ultra-Short Waves].—Price, p. 325. A System for the Inversion of Frequency Distribution [for Secrecy
- and Other Purposes].—Niwa and Hayashi, p. 36.
 Secret [Telegraphic and Telephonic] Communication by Phase Modulation Method.—Kujirai and Sakamoto, p. 35.

- A Bridge Type Speech Inverter [for Secret Radio-telephony] .---Matsuyuki, p. 36.
- Secret Telephony: the Application of "Kinematic Distortion" in Sound-on-Film and Magnetic Systems.—Podliasky, p. 155. Multiplex Working and Its Application to Secret Telephony.—
- Villen, p. 342. Short-Wave Circuit emitting Trains of Waves at Equal Intervals
- of Time [and Possible Applications].—Perrucci, p. 391. The Proof of the Shot Effect by the Building-Up of Oscillations in a Valve Generator.—Hässler, p. 619. The Single Side-Band System applied to Short-Wave Telephone Lieber Portreera.
- Links.—Reeves, p. 391. Arrangement for Single Side-Band Modulation.—von Plebanski,
- p. 446. Single Side-Band Telephony on Short Waves .- Deloraine : Reeves,
- Single Side-Band Telephony on Short Waves.— Delorathe : Reeves, p. 446.
 Single Side-Band Radiotelephony [Theory and Methods, including Balanced Modulation by Diodes].—Kolesnikov, p. 565.
 The Stabilisation of High Frequency Generators [Survey, for International Electricity Conference].—Kiebitz, p. 37.
 Standing Wave : see under Ultra-Short.
 Damped Waves, Musical Spark Transmissions, Long Waves, Arcs and Alternators I. Survey of Tan Yareni.— Botherout p. 295.
- and Alternators [a Survey of Ten Years].—Bethenod, p. 325. Study of the Synchronisation of a Self-Excited Oscillator, and of
- Subra, Its Behaviour in the Neighbourhood of Synchronisation.-Its Behaviour in the Neighbourhood of Synchronisation.—Subra, p. 619. Telephony by Carrier and One Side Band.—Chakravarti, p. 502. A Sensitive Tuning Indicator [Dry-Plate Rectifier Disc and Milli-ammeter shunted by Condenser].—Blitch, p. 446. Studies on Radiotelephone Transmitters and Receivers for Ultra-Short Waves.—Ataka, p. 501. On the Modulation of an Ultra-Short Wave by a [Modulated] Medium Wave and its Detection.—Ataka n. 620.

- Medium Wave, and its Detection.—Ataka, p. 620. The Waves of Less Than Ten Metres [Ultra-Short Waves : a Survey
- of Ten Years].—Beauvais, p. 325. Electron Conduction in Thermionic Valves [and the Generation of Ultra-High Frequencies in Diodes].—Benham: Potapenko,
- p. 444.
 Discussion on "A New Circuit for the Production of Ultra-Short-Wave Oscillations."—Cartara : Kozanowski, p. 211.
 The Generation of "Centimetre" [Ultra-Short] Waves.—Chapman,
- p. 37.
- p. 37.
 p. 37.
 p. 37.
 p. 37.
 p. 32.
 p. 32.

- Short-Wave Bahd).—Grimit, p. 445.
 Sinort-Wave Bahd).—Grimit, p. 445.
 Five-and-Ten " [Uftra-Short-Wave] Oscillator-Amplifier Transmitters.—Griffin, p. 620.
 Oscillators for Very High Frequencies and Radio-Communication on Ultra-Short Waves [A Survey].—Gutton, pp. 37 and 324.
 New Transmitter and Receiver for Ultra-Short Waves [Grid and Anode led out through Both Sides of Bulb, for use with Two Lecher Wire Systems].—Hollmann, p. 99.
 The Ultradynamic Excitation of Oscillation by Retroaction of "Inversions" Theory of Ultra-Short Wave Generation by Normal and Retarding-Field Circuits].—Hollmann, p. 563.
 Magnetostatic Oscillators for Generation of Ultra-Short Waves.—Kilgore, p. 154: see also Mouromtseff, below.
 The Use of Insulated Reflection Plates, sliding on Parallel-Wire Supply Leads, in place of Choking Coils in Ultra-Short-Wave Work.—Kohl, p. 445.
 On the Production of Undamped Oscillations of [Ultra-Short] Wavelengths of the Order of a Decimeter in a Reaction Circuit. Part 1.—Kroebel, p. 36.

- Wavelengths of the Order of a Decimeter in a Reaction Circuit. Part I.—Kroebel, p. 36.
 The Tool-Box 56-Mc [Ultra-Short-Wave] Transceiver: a Hand-Portable Five-Metre Station with a New Type [Pickard] Antenna System.—Leonard and Hadlock, p. 620.
 Production of Electronic [Ultra-Short-Wave] Oscillations with a Two-Electrode Valve.—McPetrie, p. 390.
 A [Split-Anode] Magnetron Oscillator for Ultra-Short Wavelengths. —Megaw, p. 324.
 Electronic Oscillations. Also An Investigation of the Magnetron [Ultra-] Short-Wave Oscillator. Production of Electronic Oscillator. [Ultra-] Short-Wave Oscillator. Production of Electronic Oscillations [Ultra-Short-Wave Oscillator] and a Comparison between Electronic and Dynatron Oscillator [and a Comparison between Electronic and Dynatron Oscillations].

- [and a Comparison between Electronic and Dynatron Oscilla-tions].-Megaw: General Electric Company, p. 270. On the Intensity of Electron [Ultra-Short-Wave] Oscillation in a Triode.-Morita, pp. 154 and 501. Magnetostatic Oscillator for [Ultra-Short] Waves below 50 Centi-metres.-Mouromtseff and Kilgore, p. 98: see also Kilgore. The Generation of Standing Waves [Ultra-Short] Waves down to 3 Metres, using Concentric Feeders in the Oscillating Circuit].--Mouromtseff and Noble, p. 98.

Transmission.

- New Forms of [Ultra-] Short-Wave Tubes [including the "Standing Wave" and "Magnetostatic" Oscillators].—Mouromtseff, Kilgore and Noble, p. 98.
- Electronic [Ultra-Short-Wave] Oscillations in a High Vacuum [Electronic [Ultra-Short-Wave] Oscillations in a High Vacuum [Electron Flow equivalent to Negative Resistance for a Certain Frequency Band].—Müller, p. 443. On the Production of Ultra-Short-Wave Oscillation with a Cold-Cathode Discharge Tube [and Strong Magnetic Field].—Okabe,
- p. 501.

- The Use of Magnetic Fields for the Production of Ultra-Short Waves. Magnetron Transmitters.—Ponte, p. 444. On the Generation of Ultra-Short Electromagnetic Waves using the Scheme of H. Barkhausen and K. Kurz.—Potapenko, p. 99 : see
- Scheme of R. Barriausen and R. State and R. State and S. State and S.
- Curved Connector of Length Chosen to get Ultra-Short] Waves RCA, p. 620. A New Spark Oscillator for Decimetre [Ultra-Short] Waves [Concentric Tube Circuit Design, for Greatly Increased Powers]. —Rohde and Schwarz, p. 501. Electron [Ultra-Short-Wave] Oscillations.—Rostagni, pp. 37 and
- Short- and Ultra-Short-Wave Transmitting Circuit with Several Lecher Pairs of Mica-Insulated Copper Strip.—Rothe and Roosenstein, p. 211.
 The Generation of Hertzian Waves [including Ultra-Short Waves] by means of Diodes.—Sahánek, p. 36.
 Ultra-Short-Wave Technique in Radio Communication.—Smith-Rose no 00

- Rose, p. 99. S.F.R. Ultra-Short-Wave System using Magnetrons [for Wave-lengths 70-120 cm].—Soc. Française Radio-Electrique, p. 390. Crystal Control of Ultra-Short-Wave Transmitters.—Anon.:
- Straubel, p. 37. Points of Connection of Feeders to Lecher System in Ultra-Short-

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 The Generation of Ultra-Short Waves by Magnetron Oscillators with Multiple Filaments.—Uda, Ochiai and Seki, p. 501.
 Circuit for Generating Ultra-Short Waves below 1 Metre with an Output of 5 Watts and Over [Oscillatory Circuit between Anode and Cathode].—Westinghouse Company, p. 154.
 100 Metres and Below [Survey of Methods of Generation of Ultra-Short Waves].—Whitehead, p. 390.
 The Setting-In of Ultra-High-Frequency Oscillations.—Witt, p. 98.
 Comparison between Push-Pull Connected and Parallel Connected Types of Electron Oscillation [Ultra-Short-Wave] Circuits.— Vamauchi, p. 501.

- Yamauchi, p. 501. Slightly Damped Ultra-Short Electric Waves [below 10 cm : Experimental Method of Generation]. Zakrzewski and Miesowicz, p. 564. Self-Modulation of Barkhausen-Kurz Ultra-Short-Wave Trans-

- Self-Modulation of Barkhausen-Kurz Ultra-Short-Wave Transmitters, p. 99.
 [Ultra P] Short-Wave Generating Circuit using Valve with Two Cold Electrodes, Point and Plate, p. 99.
 Ultra-Short and Ultra-High: see also Barkhausen, Electron, Micro-Waves, Screen-Grid, Very Short.
 A Method of Obtaining Very Low Frequency Alternating Currents by means of a Series-Wound D.C. Dynamo [combined with a Separately-Excited Dynamo acting as a Condenser].--Hueter, n. 38
- p. 36. Radio Communication by means of Very Short Electric Waves. Marconi, p. 153.

RECEPTION

- A Variable Wavelength Aerial [Aerial Wire winding on Metal Drum: Improved Short-Wave Reception by Adjusting to Optimum Natural Wavelength], p. 566.
 A Crystal Control Superheterodyne Receiver [for Aeroplanes: Western Electric 12A Receiver] Fischer, p. 504.

- Western Electric 12A Receiver].—Fischer, p. 504.
 Airplane Radio Freed from Ignition Interference.—Jenkins, p. 215.
 New Ideas in American Sets, p. 100.
 A Review of Developments in [American] Broadcast Receivers of 1993.—Messing and Cohen, p. 623.
 A High-Output Amplifier [Attachment] for the Battery Receiver : Improved Performance from Battery Sets—An Application for the New Class B Audio Tube.—de Soto, p. 39.
 Amplifiers for Bands of Frequencies (for Frequency-Changing Receivers).—Drouin, p. 37.
 High-Frequency Amplifier with Series Resonant Circuit [as Plate Load instead of Usual Parallel Resonant Circuit : Improved Results in Amplification and Stability, e.g. in I.F. Amplifier of Superheterodyne Receiver].—Iso, p. 504.
 Note on Tuned-Anode and Transformer-Coupled R.F. Amplifiers.— Marique, p. 393.

- Note on luned-Anote and transformer coupled the Coupling : for Marique, p. 393. A New Type of L.F. Amplifier [Glow-Discharge Tube Coupling : for Frequencies from 0 to 10 000 0/s[.—Schäfer : Peek, p. 212. H.F. Amplifier with High Amplifying Power [Reduction of Anode-Circuit Damping in a S.G. Stage without Alteration of Tuning].—
- von Ardenne, p. 566. A Regenerative Resistance Amplifier for a Wide Frequency Band.— Wada, p. 99.

- Amplifiers : see also under " Properties of Circuits," " Acoustics "
- Amplifiers : see also under "Properties of Circuits," "Acoustics" and "Subsidiary Apparatus." New Auto Radio Receiver [Nine-Valve Superheterodyne with Class B Amplification].—RCA Victor Company, p. 100. Auto-Radio an Expanding Market in 1933 : Police Radio Increases, p. 214 : see also Police. Eliminating Spark Plug Disturbance in Automobile Radio.— Marsten, p. 325. Automatic Disconnection of Mains Aerial on plugging in the Outside Aerial in a Telefunken Receiver, p. 100

- Automatic Fading Compensation.—Nentwig, p. 158. Automatic Fading Regulation without Regulating Valve or Battery.

- Automatic Fading Regulation without Regulating Valve or Battery. —Franck, p. 693.
 Automatic Gain Control of Radio Receivers [on Commercial Channels].—Cohen, p. 393.
 Automatic Gain or Volume Control : see also Fading, Volume.
 Automatic Regeneration [One Adjustment gives Suitable Re-generation Constant over Whole Tuning Scale].—Tanner, p. 566.
 Circuits for Amplified Automatic Volume Control [using the Duplex Diode Triode].—Barton : Travis, p. 213.
 Practical Automatic Volume Control to the Monodial.—Cocking, p. 272.

- Accung Automatic volume control of the p. 272. Delayed Amplified A.V.C.—Cocking, p. 623. Delayed Diode A.V.C.—Cocking, p. 623. Corrected A.V.C.—Cossor Laboratories, p. 447. Automatic Volume Control for Radio Receivers [Survey of American Developmentel Richer, n. 447.
- Automatic Volume control for Kaulo Accelvers (Survey of American Developments) Fisher, p. 447. Cutting Out Distorted Reception of Over-Weak Signals in Receivers with A.V.C., with Help of Thyratron controlled by A.V.C. Rectifier.—RCA, p. 567. Automatic Volume Control for Selective Fading by Subdivision of Encourser. Rend into Source Compension scot with its of
- Frequency Band into Several Components each with its own Control Frequency.—Siemens and Halske, p. 567.

- Artequency band into Several Components each with its own Control Frequency.—Siemens and Halske, p. 567.
 Automatic Volume Control.—Smith, p. 158.
 An A.V.C. Unit.—Smith, p. 326.
 Automatic Volume Control [with Double-Diode Triode, giving Quiet, Amplified and Delayed AVC].—Smyth, p. 213.
 Automatic Volume Control by Regulation of Filament Current, which forms Anode Current of Control Valve.—Telefunken Company, p. 158.
 Automatic Volume Control and Fading Compensation [Survey of New Methods and Possibilities].—Wigand, p. 567.
 Adding Automatic Volume Control to an Existing Receiver with a Variable-Mu H.F. Stage, p. 213.
 The History of A.V.C., p. 326.
 Balancing Radio Receiving Circuits [Discussion of Methods of Stabilising against Oscillation].—Tennil, p. 100.
 Flexible Band Pass Unit.—Dent, p. 39.
 The Use of Uranium Dioxide as a Series Resistance for Iron Barretters.—Meyer, p. 273.

Barretters.—Meyer, p. 273. he Beat-Note-Combinational-Tone Controversy.—Hazel and

- The
- The Beat-Note-Combinational-Tone Controversy. Inact and Ramsey, p. 623. Receiver Scales at the Berlin Radio Show, in particular the AEG "Optical Station Indicator," p. 39. Receivers at the Berlin Radio Show.—Schwandt, p. 39. The Present Position in Broadcast Receiver Design [Berlin Ex-bilition and Vianas Autumn Fair 1032.—Klein Mittelmann,

hibition and Vienna Autumn Fair, 1932 .- Klein : Mittelmann,

- p. 100. New Automatic Bias Scheme Bowen, p. 213. Future Trends in Broadcast Receivers : Possible New Gadgets.
- Jarvis, p. 156. The Design of Broadcast Receivers.—Turner, p. 156. Broadcasting and Current Supply [Statistics regarding Increased Power Consumption due to Broadcasting].—Civita, p. 393. New Battery Output Stage: Class B Amplification: the Latest Development.—Walker, p. 272. Class "B" Economy is Two-Fold.—Scroggie, p. 505. Controls for 1933 Receivers [particularly Moulded Carbon Variable Resistances and Their Uses].—Wunderlich, p. 447. Copper-Oxide Rectifier used for Radio Detection and Automatic Volume Control.—Grondahl and Place, p. 39. A New Method of Radioelectric Coupling: the "Diffusion" Coupling.—Cordebas, p. 622. Reception in China on a Grystal Detector [Nanking at 500 km by day: Manila at 2 500 km by night].—Oster, p. 446. Decoupling Efficiency [and a Convenient Alignment Chart].— Barclay, p. 504.

- Barclay, p. 504.
- Barclay, p. 304.
 Decoupling and Instability [Production of Motor-Boating by Incorrect Design of Decoupling Circuits].—Preston, p. 448.
 The Optimum Decrement of Tuned Circuits for the Reception of Telephony [with Channels spaced 9 kc/s].—Bell, p. 503.
 Method of Demodulating a Frequency-Modulated Wave.—RCA, p. 273.
- p. 273. Some Notes on Demodulation .--Roder, p. 212.
- Demodulation : see also Detection. Double-Grid Valve in Circuit to prevent Overloading [Anode-Bend
- Rectification] in Grid Detection, p. 100. Theory of the Detection of Two Modulated Waves by a Linear Rectifier.—Aiken, p. 392.

Reception.

The Mode of Action of Diode Detection.—Urtel, p. 623. An Analysis of Power [Grid] Detection [and the Use of a High-Impedance Choke in place of the Grid Leak and of a Tungsten Lamp as Plate Series Resistance].—de Cola, p. 566.

Detection : see also Demodulation. Screen-Grid Voltage and Detector Sensitivity.—Flippin, p. 38.

The Detector.—Lewis, p. 38. Improving the Grid-Leak Detector : a Simple Method of Obtaining Greater Linearity in a Superheterodyne Receiver [Addition of Second R.F. Choke between Anode and Junction of By-Pass Condenser and R.F. First Choke].—Smith, p. 100. he H.F. Screen-Grid Valve as an Anode-Bend Detector.—

Condenser and Annu Alexandrow Valve as an Anous some Kammerloher, p. 623. The H.F. Screen-Grid Valve as an Anous some Functions of the Leaky-Grid Detector with Reaction, divided between Two Valves, p. 157. The Diode Rectifier].—Smith, p. 39. Some Notes on the Use of a Diode as a Cumulative Grid Rectifier.— Biedermann, p. 326. Biode Detection Analysis.—Kilgour and Glessner, p. 566. Cocking, p. 39.

The Tuning Curves of Electrical Distant Control Devices for Radio Receivers ---Schadow, p. 39.

Receivers.—Schadow, p. 39. Pass Filters].—Howe, p. 623, Voltage Amplification with High Selectivity by means of t Dynatron Circuit.—Colebrook, pp. 212 and 326. Trends of Design at the Ninth Radio Exhibition, Paris, 1932. by means of the

Adam, p. 155. The Radio Exhibitions [National and International] in Paris, 1932, p. 505.

Exhibitions: see also Berlin, Radio, Trend, and under "Miscellaneous."

"Miscellaneous." The Introduction, into an Existing Receiver, of Exponential Valves in the place of ordinary Screen-Grid Valves, p. 446. Anti-Fading Circuit using Variable-Mu Valve.—Chrétien, p. 100. Anti-Fading Circuits.—Chrétien, p. 158. Counteracting Fading by Periodic Detuning of Receiver.—Deutsche Tel:werke u. Kabelind. A.G., p. 214. The Influence of Fading Compensation on Contrast in Music.— Sturm a 623.

Sturm, p. 623. The New Tuning Coils ["Ferrocart" Iron Cores].—Sowerby : Vogt, p. 39.

Frocart, a New Material [and a Two-Valve Receiver using Ferro-cart Coils].—Olvenstedt, p. 100. Iron Powder Compound Cores for Coils [Ferrocart, etc.].—G.W.O.H.

Iron Powder Compound Cores for COIS Ferrocart, etc.].—G.W.U.H. p. 173.
The Ferrocart III.—Cocking, p. 273.
Class "B" Ferrocart Receiver.—Page, p. 326.
Iron-Content [Ferrocart] Cores for High-Frequency Coils.—Schneider, p. 403.
Ferrocart : see also under "Subsidiary Apparatus and Materials."
Fidelity Compensation by Regeneration [by Feeding-back Part of Output in Phase to Screen-Grid Circuit of Tetrode].—Matthews, p. 212. p. 212.

Coupling Coils tending to Neutralise the Fixed Couplings.— Neissner, p. 566. The Best Filter Chain for Mains-Driven Apparatus.—Piesch, p. 158. Filter for the Intermediate-Frequency Amplifier [of a Superhetero-dyne Receiver].—Piesch, p. 21. Square-Top Filters [especially for the I.F. Circuits of Super-heterodyne Receivers].—Piesch, p. 504. French Receivers].—Piesch, p. 504. Retaining Higher Frequencies: Part II. Frequency Correction.— Bowen, p. 99. See also Tone Correction. Glow-Discharge Tube between Grid and Anode of Reaction Audion to prevent Adjustment beyond Oscillation Threshold.— Hinrichsen, p. 272. Hinrichsen, p. 272.

An Obscure Cause of Poor Reception [Faulty Combination of Parallel-Feed Transformer and Automatic Grid Bias Resistor].--

Parallel-Feed Transformer and Automatic Grid Bias Resistor].— M. G. Scroggie, p. 213.
High-Selectivity Tone-Corrected Circuits.—Robinson: G.W.O.H., pp. 99 and 156.
Wireless in the Modern Hotel [Waldorf Astoria].—Dinsdale, p. 39.
Suppression of Mains Hum: the Use of an Auxiliary Valve in Opposition to Output Valve of a Bridge Circuit: of Rectifiers in Opposition across Heating Circuit.—Siemens. Schukert, p. 448.
Bridge-Type Push-Pull Amplifiers [to avoid Hum induced in Coupling Transformer].—Tulauskas, p. 504.
Ingenions Circuits in New Radio Receivers, p. 100.
Study of the Input Circuit of a Radiotelephonic Receiver [and the Predominant Importance of the H.F. Losses].—Mezey, p. 448.
Various Methods of Detecting Faulty Insulators on H.T. Lines under Tension.—Robertson, p. 392.
The Law of the Broadcast Listener and the Elimination of Wireless Interference.—Adam, p. 157.

Interference.—Adam, p. 157. Concerning the Second Congress of Defence against Radioelectric Interference (Paris, 25th-27th November, 1932).—Adam, p. 325.

Fundamental Points in the Suppression of Radio Interference [Man-Made].—Alexander, p. 392. Interference with Wireless Reception Arising from the Operation

Interference with Wireless Reception Arising from the Operation of Electrical Plant.—Angwin, p. 39.
 The Radio-Noise Meter and Its Application to the Measurement of Radio Interference.—Barhydt, p. 392.
 Eliminating Radio Interference from Pin Type Insulators.—Barrow, p. 325.
 Avoidable Interference.—Bernaert, p. 505.
 Antenna Transmission Line Systems for Radio Reception [Elimination of Man-Made Interference by Suitable Location of Acrial and the Use of a Shielded Lead-In].—Brightam, p. 449.
 Cutting Out the Crackle : What the Listener Can Do to Minimise Interference.—Chin, p. 40.
 Whistle Suppressor [A Simple Tuned Filter for Eliminating Heterodyne Interference].—Cocking, p. 39.
 Thefference with Broadcast Reception due to Mercury-Vapour Rectifiers.—Dennhardt, p. 391.
 The Construction of Choking Coils for Preventing Radio Interference

Rectimers.—Dennhardt, p. 391. The Construction of Choking Coils for Preventing Radio Inter-ference [e.g. from Mercury Vapour Rectifiers].—Glas, p. 39. Interference : Notes on Methods for Elimination of Interference caused by Non-Radio Devices.—Glas, p. 157. Interference with Broadcast Reception.—G.W.O.H., p. 447. Devices to prevent Man-Made Interference with Radio Reception, and Their Use. Memory and Thereference with Radio Reception,

and Their Use.—Hémardinquer, p. 157. The Effect of the Leads to an Interference-Suppressing Condenser.-

Kotowski and Kühn, p. 325.

Action Reception and Interference from Neighbours [from Electrical Apparatus, etc.].—Mestre, p. 325. Problems of Electrical Interference,—Morris, p. 623. Interference with Broadcast Reception.—Nat. Elec. Light Assoc., p. 447.

The Legal Position of Producers of Wireless Interference with

The Legal Position of Producers of Wireless Interference with respect to the Listeners.—Ottoz, p. 158. [Hints on] Reducing Noise Interference [including the Limited Usefulness of the Shielded Lead-In].—Philos Company, p. 325. Anti-Interference Filter for Electric Motors, etc., which does not raise Potential of Frame of Motor.—Philips' Company, p. 325. An Apparatus for Measuring the [Radio-] Frequency Spectrum of Sources of Interference with Broadcast Reception.—Wild : Siemens and Halske, p. 272. Some Causes of Interference with Radio Reception on Aeroplanes, and Methods of Overcoming Their Effects.—Zanini, p. 100. Interference Filtering [Special Wave Trap Circuit], p. 157. Electrical Interference [Additional Causes, including Static Charge on Motor Frame due to Belt Slippage], p. 39. Interference : see also Noise, Screened, Superhet, and under "Aerials."

Aerials Italian Broadcast Receivers : " Radiomarelli " 1932-33 Receivers,

P. 623. Broadcasting Progress in 1932, and European Broadcasting versus Economic Depression [U.I.R. Statistics of Listeners].—Burrows,

An Improved Version of the Loftin-White Circuit [using only Indirectly-Heated Valves, including a Pentode in the Output

273.

p. 273. VDE Regulations for Mains-Driven Broadcast Receivers.—Verband Deutscher Elektrotechniker, p. 326. The Influence of Matching [Circuits with Valves] on the Ampli-fication and Selectivity of Tuned R.F. Amplifiers.—Baerwald, p. 503.

p. 5005. Matching : see also under "Properties of Circuits " and " Aerials." An Alf-Wave [Two-Valve] Midget Receiver: a Semi-Portable covering from 12 to 4 500 Metres.—Parmenter, p. 100. The Midget Universal Mains Set.—Keith Henney, p. 273. The Modern D.C. Three [with Screen-Grid Detector].—Page, p. 157. The Production of Negative Conductances by means of Retroactive Couplings [and the Calculation of Retroactive Receiver Circuits]. —Kantter, p. 447.

- Couplings [and the Calculation of Retroactive Receiver Circuits]. —Kauter, p. 447. Suppression of Noise in Radio Receivers : QAVC [Quiet Automatic Volume Control], NSC [Noise Suppression Control], or simply "Squelch."—Messing, p. 328. An Inter-Carrier Noise Suppression System [using the Wunderlich Valve of a New Type, with Small Shielded Extra Anode].— Wunderlich, p. 447. Noise Intensity in Radio Reception.—Byrne, p. 448. Inter-Carrier Noise Suppression : a New System [using the Wunder-lich B Valve and Automatic Volume Control].—Wunderlich, p. 213

p. 213.

Maximum Output, Efficiency, and Optimum External Resistance of Output Valves [for Class A and Class B Amplification].--Urtel, Output V

Output Varyes for One of Combined Oscillator-Detector for Super-heterodyne Receivers].—Lyons, pp. 394 and 504.
 Improvements to the Pentode Output Stage [Reduction of Capacity in Choke Filter Output Circuit].—Piesch : Sims, p. 157.
 The "People's Receiver," pp. 505 and 567.

Stagel – Prinzler, p. 100. The H.F. Currents produced by H.T. Magnetos.—Jafray, p. 271. Superheterodyne Receiver with Magnetostrictive Coupling in I.F. Circuit to increase Selectivity.—USSR Electrot. Association,

Reception.

- Reception Tests on the German "People's Receiver "-Leithauser, p. 623.
- New Development in Tuning ["Permeability " Tuning] .-Α Hallows, p. 100. Permeability Tuning.—Scroggie, p. 158. Ferro-Inductors and Permeability Tuning.—Polydoroff, p. 393. The Development of Police Motor-Car Radio.—Thomas, p. 327:

- see also Auto.
- Back to Quality in Radio Receivers! [With Curves showing Wide Difference in Tone Fidelity between Large and Small Receivers]. p. 447.

- p. 447.
 Outstanding Battery Set Development ["Quiescent Push-Pull "].— Yeoman Robinson, p. 156.
 The Quiescent Push-Pull Two.—Page, p. 156.
 New Apparatus and Appliances [Special Transformer and Output Choke for "Quiescent Push-Pull "], p. 213.
 Q.P.P. with Triodes.—Page, p. 213.
 Practical Hints on Q.P.P.—Hallows, p. 504.
 Present and Possible Future Trends in Radio, p. 326.
 Radio Receiver Situation for 1933 [including "Colour" Visual . Indication of Noise, Tone and Volume Control], p. 447.
 Radio at the Leipzig Spring Fair, p. 447.
 Trends in Radio Design and Manufacturing, p. 580.
 Radio Distribution System for Apartment Buildings.—Bell Labora-tories, p. 567.

- Radio Distribution System for Apartment Buildings.—Bell Laboratories, p. 567.
 A Radio Distribution System for Apartment Buildings.—Bell Laboratories, p. 567.
 A Radio Distribution System for Apartment Buildings [wired with Special Coaxial Conductor: One Aerial, 3000 or more Receiver_Bell, p. 326.
 The Radio Industry in the Season 1932/1933 [Analysis of Types, Prices and Sales].—Menzl, p. 214.
 Radio Receiver Design [The Equivalent Circuits Useful in Broadcast Receiver Design].—Smith, p. 447.
 The Use of Instruments in Radio Receiver Manufesturia-Miller, p. 447.

- Miller, p. 447.

- Radio Statistics—Production and Use, p. 326. Receivers [a Survey of Ten Years].—David, p. 326. Discussion on "Some Notes on Grid Circuit and Diode Rectification" Discussion on "Some Notes on Grid Circuit and Diode Rectification " [Distortion avoided even for 100% Modulation by connecting Grid Leak to Positive Point instead of to Earth.]—Kelly: Nelson: Terman, pp. 213 and 392. Refex Circuit Considerations.—Stinchfield and Schade, p. 567. The Use of Multi-Wave Circuits in Grid and Anode Circuits of a Receiver with Retroaction, to give Rectangular Resonance Curre.—Lorenz, p. 448. The Retarding-Field Audion controlled without Power Expenditure [and used for Waves other than Ultra-Short].—Hollmann, p. 621: see also Ultra-Short. The Action of Damping Reduction [by Retroaction] in Broadcast Receivers.—Kautter, p. 622. Alteration of Tuning when the Retroaction Coupling is Varied.— Schienemann, p. 622.

- pp. 99 and 157.

- Screened Aerial Down Leads.—Brigham, p. 325. Reducing Man-Made Static [The Use of a Screened Lead-In and the Calculation of the Appropriate Impedance-Matching Network].
- Browning, p. 157. The Question of the Screened Aerial Lead [and the Recommenda-tions of the Association of German Electricity Works].—Nentwig, p. 157.
- Screened Cable for Down Lead [Capacity under 30[cm/m: Weight 160 gm/m].—Telefunken Company, p. 325. The Installation of Aerials with Screened Down Leads.—Wigand,
- p. 449.

- p. 449.
 Why Does the Low-Frequency Amplifier How!? Tests on the Static Screening of A.F. Transformers.—Piesch, p. 448.
 Second Channel Suppression.—Kinross, p. 446.
 A Practical Criterion of Selectivity [Unsatisfactory Nature of I.R.E. Practice and of Thomas' Method: Need of Arbitrary Limit defining "Just Appreciable" Interference: Suggestion of 10 % Relative Audio Volts Output].—Callendar, p. 100.
 Selectivity in Broadcast Reception. 1. Band-Pass Filters. 2. Tone Correction.—Davidson: Bell, p. 326.
 Average Selectivity Curves of 1931-32 Superheterodyne and Tuned R.F. Receivers.—Horn, p. 326.
 The Representation of [Single-Peak] Resonance Curves by "Selectivity Inderes."—Kafka, p. 448.
 Systematic Study of Short-Wave Triode Amplifying Circuits by "Neutralisation" [particularly the Bridge Method].—Haraguchi, p. 38.

- guchi, p. 39.
- Short-Wave Two [with Screen-Grid Valve as Regenerative De-tector].—Dent, p. 39.
- Short-Wave Transoceanic Telephone Receiving Equipment .-
- Short-Wave Transoceanic Telephone receiving Equipment Polkinghorn, p. 327.
 Practical Short-Wave Reception.—Whitehead, p. 393.
 Universal A.C. Short-Wave Converter.—Cocking, p. 393.
 An A.C. Short-Wave One-Valve Receiver [using a Pentode : Smooth Reaction down to 10 Metres], p. 505.

High-Speed Telegraphic Reception on Short-Wave Transoceanic Services [with particular reference to the "Double Undulator" System for Combating Fading and Atmospherics].—Mögel, p. 503.

p. 503. The Radio Receiver Characteristics related to the Sidehand Coefficient of the Resonance Circuit.—Takamura, pp. 38 and 156. Sidehand Splash.—Hallows, p. 157. A Long-Wave Single-Sidehand Telephony Receiver for Trans-atlantic Working : Hill and Page, p. 566. Improved Smoothing in Mains Receivers by connecting Valves as Series Elements of Anode-Current Filter Chain.—TKD, p. 448. The Problem of Stability [in Radio Receivers].—Chrétien, p. 448. Stability Replayme of Tuned P. E. and Superheteredme Receivers

- Stability Problems of Tuned R.F. and Superheterodyne Receivers.
- Place, p. 623. A Superheterodyne Receiver with Several Frequency Changes in the I.F. Circuit.—Aigner, p. 566.

- p. 623.

- Monodial D.C. Super.—Cocking, p. 100. The All-Wave Monodial Super.—Cocking, p. 213. The New Monodial Super.—Cocking, p. 504. New Ideas for the Superheterodyne (including the Pentagrid Valve
- Arew fields for the Superheterodyne [Including the Peritagrid Valve as Frequency Changer].—Cocking, p. 504.
 The Di-Super-6 [Superheterodyne] Receiver with Double Frequency Change [avoiding "Double Image"] Trouble without Defects of Usual Methods].—De Giorgi, p. 39.
 Straight Sets versus Superheterodynes : Correspondence.—Elliott, 2000
- p. 326. A Note on Interference Tones in Superheterodyne Receivers.—Floyd,
- p. 504.
- p. oor.
 Papers on the "Single-Signal "Superheterodyne Receiver.—Lamb, pp. 39, 327, 446 and 504.
 The Single-Signal Receiver at Work : The Single-Signal Super in Another Dress.—Parmenter : Lusk : Lamb, p. 101.
 A Superheterodyne Receiver using the New "Fading Hexode " and "Mixing Hexode "Valves.—Wigand : Telefunken, p. 446.
 Server Grid Valve Duractere Oreilbarte Circuit for the term
- "Mixing Hexode " Valves.—Wigand : Telefunken, p. 446. A Screen-Grid-Valves.—Wigand : Telefunken, p. 446. A Screen-Grid-Valve Dynatron Oscillator Circuit for Superhetero-dynes, Free from Harmonics, p. 157. The "Die Sendung " 5-Valve Superheterodyne Receiver [with only one 1.F. stage : A utomatic Volume Control], p. 100. On Super-Regeneration.—Egerland, p. 99. The Theorem of the Generative Counciling Combine of Con-tine Theorem of the Council Control of the Council of the Counci

- On Super-Regeneration.—Ligerland, p. 99. The Theory of the Super-Regenerative Coupling.—Gorelik, p. 622. A Super-Regenerative Short-Wave Attachment [for Telephony Reception], p. 393. Transforming Receiver Constructional Diagrams to work from Different Supply Sources [A.C., D.C. and Battery].—Schwandt,
- p. 158. "Synchronous" Reception.—de Bellescize, p. 38.

- "Synchronous" Reception.—de Bellescize, p. 38.
 Tatsfield Relaying Receivers, p. 393.
 Receiver Testing Equipment for Shop or Field.—Myers, p. 158.
 Set Analysers [for Testing Broadcast Receivers].—Lewis, p. 393.
 A Note on the Theory and Practice of Tone-Correction...-Colebrook, pp. 156 and 504. See also Frequency. High Selectivity.
 Remarks on "A Note on the Theory and Practice of Tone-Correction". [Additional Method depending on Series Resonant Circuit].—Cope: Colebrook, p. 504.
 Tuned-Transformer Coupling Circuits [Low-Loss Air-Core Transformers, as used in I.F. Amplifier of Field Strength Measuring Set].—Christopher, p. 328.
 Transformeless Plate Supplies [for Receiver Valves], p. 504.
 The Trend of Progress, p. 623.
 Receiving Sets for the Tropics : a Plea for Study of the Eastern Market, p. 504.

- Market, p. 504.
- Tuning Discontinuities of a Rotating Variometer smoothed out by Combination with a Rotating Condenser with Wave-Form Edges.
- —Telefunken, p. 448. Gaseous Discharge Tubes for Radio Receiver Use [as Visual Tuning Indicator with or without "Noise Gate"].—Dreyer : Senauke, p. 272.

- p. 272.
 The Two-Circuit Tuner [in Broadcast Receivers: Usual Adjustment of Coupling loses Brilliancy of High Notes: Desirability of Small Amount of Adjustable Tone Correction].—Editorial, p. 99.
 Improving the 50-Mc Reteiver: Constructional Details of Two New Sets for the Ultra-High Frequencies.—Hadlock, p. 447.
 The Rectification of Alternating Voltages at Ultra-High Frequencies by means of Diodes.—Carrara, p. 503.
 Studies on Radiotelephone Transmitters and Receivers for Ultra-Short Waves [and the Super-regenerative Action of an ordinary Regenerative Receiver].—Ataka, p. 501.
 On the Modulation of an Ultra-Short Wave by a [Modulated] Medium Wave, and its Detection.—Ataka, p. 620.
 The Detection of Microwaves [Ultra-Short Waves of Frequency about 10° c/s].—Carrara, p. 38.
 Ultra-Short-Wave Two.—Dent, p. 447.

Reception

- An Unusual 56Mc [Ultra-Short-Wave] Super-Regenerative Re-ceiver : Details of a Portable Set with Self-Quenching Detector.— Haydock, p. 567. Reception of Ultra-Short (3 Metre) Waves on a Tourmalin-Stabilised
- Receiver.—Heinrich-Hertz Institute, p. 622. The Reception of Decimetre [Ultra-Short] Waves with the Re-tarding-Field Audion.—Hollmann, p. 621 : see also Retarding-Field.
- Receiver for **Ultra-Short** Waves, using Split-Anode Magnetron.— Int. Gen. Elec. Company, p. 273. Oscillating Split-Anode Magnetron as Detector for **Ultra-Short** Waves.—Int. Gen. Elec. Company, p. 326. Experiments on the Reception of **Ultra-Short** Waves.—Marconi,
- p. 155.
- Witra-Short : see also Ultra-High.
 Visual Test Devices [giving R.F. Frequency Response Curve of Receiver or Components, for Production Testing : Rotating Sweep Condenser and Mirror, Mirror Galvanometer, etc.].—
- Sweep Condenser and Mirror, Mirror Galvanometer, etc.,... Schuck, p. 38. Acoustically Compensated Volume Control for Radio and Phono-graph Sets...-Wolff and Cornell, p. 332. Manual Volume Controls...-Branch, p. 386. The Westeetor...-Westinghouse Company, p. 272. Wireless World Battery Baby Superhet...-Cocking, p. 39. The Wireless World Modern Battery Four...-Cocking, p. 382. The Wireless World Straight Threa (Battery, Operated)...Smith

- The Wireless World Straight Three [Battery Operated] .--Smith. p. 100.

AERIALS AND AERIAL SYSTEMS

Argument as to Reliability of Field Strength Measurements taken

- p. 624. The Improvement of Broadcasting Aerial Systems [Survey], p. 158. Is the Problem of the Communal Aerial Solved ?—Noack : Philips'

- Is the Problem of the Communit Aerial Solved (--Addack Finings Company, p. 624. The Concentrator Antenna [giving Decreased Space Wave and Increased Efficiency at the Shorter Broadcast Wavelengths].---Westinghouse Company, p. 449. Operation of the New [¹⁴ Concentrator " Directive Broadcasting] Antenna at KYW., p. 567. On the Numerical Calculation of the Current in an Antenna [and the Reduction of Related Double Integrals].--Murray, p. 215. The Distribution of Radiated Power along a Dipole [Half-Wave] Aerial --Bechmann, p. 101.

- The Distribution of Radiated Power along a Dipole [Half-Wave] Aerial.—Bechmann, p. 101.
 Asymptotic Dipole Expansions for Small Horizontal Angles.— Murray, pp. 40 and 616.
 The Generalised Theory of the Electromagnetic Field of a Dipole and of Radiation from the Latter.—Rosing, p. 40.
 Note on Directed Transmissions [from a Single, Greek-Pattern Array: the Production of Two Beams rotating in Opposite Directions by a Periodic Variation of Wavelength].—Longo, p. 505.
 Theory and Practical Application of Directed Radiation [Com-prehensive Survey of Beam Aerial Theory: Calculation of Radiation Diagram of Zeesen Short-Wave Broadcasting Aerial].— Ochmann and Rein, p. 567.
 Directive Aerial consisting of a Conductor bent into a Zig-Zag in One Plane.—International Standard Electric Corporation, p. 159.
 Phase Synchronisation in Directive Antenna Arrays, with Particular
- Phase Synchronisation in Directive Antenna Arrays, with Particular

- Phase Synchronisation in Directive Antenna Arrays, with Particular Application to the Radio Range Beacon [using the "Trans-mission Line" Antenna, Adcock Principle].—Kear, p. 625.
 Extension of the Mesny "Meandering" [Zig-zag Directive] Aerial System.—Latour, p. 159.
 Investigating the Directive Properties of an Amateur Antenna [Long L-Aerial for Short Waves].—Seaton, p. 449.
 The New High-Power Broadcasting Station at Vienna, with Re-flector Tower for Directive Working.—Telefunken, p. 215.
 Directive Actions of Wave Resonators and Their Effects on the Plane of Polarisation of Electromagnetic Waves.—Uda and Nakamura, p. 159.
 Horizontal Directive Short-Wave Antenna —U.S.S.R. Elek Ver
- Horizontal Directive Short-Wave Antenna .- U.S.S.R. Elek. Ver., p. 449.
- Improved Directive Reception on a Multiplicity of Aerials by using Repeated Frequency Multiplication before Combining.— von Plebanski, p. 328.
- von Plebanski, p. 328.
 A New Type of Directive Aerial [with Radiating Elements of Progressively Increasing Length : Especially Suitable for Ship-Shore Working].—Walmsley, p. 101.
 Short-Wave Directive Aerial Systems. Part I.—Whitehead, p. 328.
 Directive Broadcasting at WFLA-WSUN [Two Insulated Towers tuned to a Quarter Wavelength and spaced a Quarter Wavelength].—Wilmotte, p. 101.
 Directive Antennae for Broadcast Stations [particularly at WFLA, Eloridal.—Wilmotte n. 158]

- Florida].—Wilmotte, p. 158. Earth Resistances [Potential Gradient in the Surrounding Soil depends only on Dimensions of the Earth Plate].—Tagg, p. 101.

- The Resistance of **Earth** Electrodes [for Earthing Electrical In-stallations and Apparatus].—Morgan and Taylor, p. 505. Effect of the **Earth's** Non-Homogeneity in Strata on the Electro-magnetic Field of a Horizontal Transmitting Aerial [Theoretical Investigation and Experimental Confirmation on a 5.4 m Wave.]
- -Hara, p. 159. Radiation from Antennae under the Influence of the Earth's Properties. E.-Radiation into the Earth.-M. J. O. Strutt, p. 624.
- An Experimental and Analytical Investigation of Earthed Receiving
- Aerials: Corrections.—Colebrook, p. 327.
 The Effective Combating of Short Range Fading in Broadcasting, by Special Transmitting Aerial Systems [for Space-Wave Sup-

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- The Effective Combating of Near Fading in Broadcasting by Trans-mitting Aerials of Particular Design [Elektrotechnischer Verein Discussion]—Hahnemann, Harbich, Runge, Gothe, Plendl,
- Discussion].--Hannemann, Tanona, Krüger, p. 158. Field Tests on Radio Communication over Long-Distance Aircraft Routes [including the Reduction of Short-Wave Fading by Alternate-Aerial Transmission or Reception].--von Handel, Autornate-Aerial Transmission or Reception].—von Handel Krüger and Plendl, p. 557. An Anti-Fading Aerial consisting of a Wire wound into a Spiral.—

- An Antr-raump Aerial consisting of a wire wound into a spiral.— SFR, p. 273. Fading eliminated by High Aerial supported by Balloon ["Blimp Antenna"], p. 449. Anti-Fading : see also Concentrator. Cable-Type H.F. Feeders [Buried, for Transmitting and Receiving Aerial5.—Lambin, p. 567. Twisted-Pair Feeders for the Transmitting Antenna.—Grammer, p. 567
- p. 567.
- Feeders: see also Transmission Lines, Lecher Wires. On the Calculation of the [Short-Wave] Frame Antenna with Uniformly Distributed Electromotive Force.—Iwakata, p. 40.

- The Gain in Beam Antennas.—Kato and Takeuchi, p. 505. Grounds [The Use of Ground Rods], p. 40. The Electrical Heating of Overhead Lines against Hoar Frost. Halbach, p. 215. Mutual Impedance of Grounded Wires Lying On or Above the
- Surface of the Earth.—Foster, p. 624. Mutual Impedance of Long Grounded Wires when the Conductivity of the Earth varies Exponentially with Depth.—Gray, p. 327. General Formula for the Mutual Radiation Impedance of Any Straight Parts of the Wires with Standing Sinusoidal Current Distribution. Here, a 604.

- Straight Parts of the Wires with Standing Sinusoidal Current Distribution.—Hara, p. 624. The Calculation of the Impedance of Aerials [with Mid-Point Feed: for Various Values of 1/A].—Labus, p. 214. Mutual Impedance of Two Skew Antenna Wires.—Murray, p. 214. Ellipse Diagram of a Leeher Wire System [and the Transition from Double to Single Hump of Current Distribution].—Hikosaburo : Mohammed and Kantebet: Takagishi, p. 327. [Broadcast Receiving] Aerials and Lightming, p. 505. Swedish Tests on Impregnating Processes for Wooden Masts, p. 273.

- p. 273. Latitoe Masts of Tubular Construction, with Welded Joints.—Rixe, p. 394.
- Buckling Loads in Lattice Masts, particularly in High Radio Towers,

- Buckling Loads in Lattice masts, particularly in Fight Reads Content, —Föppl, p. 567.
 The Joining of Two Lines of Different Characteristic Impedance [and the Calculation of the Dissymmetric Quadripole for Match-ing a Two-Wire and a Concentric Line].—Pomey, p. 449.
 Matching Feeders with Short- [and Ultra-Short-] Wave Trans-mitting Aerials.—Issakowitsch-Kosta, p. 214.
 Radiation Characteristics of Beam Antennas [and the Dispersion of the Beam by the Heaviside Layer]: Errata.—Minohara, Tani and Ito. p. 40.
- and Ito, p. 40. The Calculation of the Radiation Characteristics and Radiation Resistances of Aerial Systems": Correction of a Formula.—
- Bechman, p. 567. Measurements on the Radiation Induction in Symmetrical [Short-Wave] Aerials [and, the Influence of Height above Ground].—
- Schmidt, p. 160. Calculation of the Radiation Resistance of a Two-Wire Feeder.-

- Calculation of the Radiation Resistance of a Two-wife Feeder.—
 Loeb: Brillouin, p. 160.
 Reply to Mr. Hallén's Remarks on my Paper "The Free Electrical Vibrations of Rod-Shaped Conductors."—Lindman, p. 101.
 A Method of Measuring the Sag of Telephone Lines [Depending on the Velocity of Propagation of a Transverse Wave].—Thomas, p. 160.
 Change of Sag due to Clearing of the Sleet on One of the Span Wires of a Suspended Overhead Transmission Line.—Nishiyama, r. 120.
- p. 160. "Receptru" Screened Lead-In Cable, p. 624. The Installation of Aerials with Screened Down-Leads.—Wigand, p. 449.
- Screened, Shielded Aerials, etc. : see also under "Reception."

Aerials and Aerial Systems.

- Antenna Transmission Line Systems for Radio Reception [Elimina-

- Antenna Transmission Line Systems for Radio Reception [Elimination of Man-Made Static by Suitable Location of Aerial and the Use of a Shielded Lead-In].—Brigham, p. 449.
 Short-Wave Aerials [for Broadcast Reception : including Frame Aerials].—Floyd, p. 40.
 Transmission-Line Feed for Short-Wave Antennas (including the Grounded Antenna].—McLean, p. 40.
 Short-Wave Aerial System with Horizontal Dipole, consisting of Two Networks of Wires, and Vertical Feeders ; for Production of Purely Horizontal Polarisation.—Telefunken, p. 158.
 Short-Wave Aerial System with All-Round Horizontal Radiation [Horizontal Radiators forming Sides of Polygon, Connected in Series by Vertical Lecher Pairs with Adjustable Bridges].— Elektroswias, Leningrad, p. 158.

- Series by Vertical Lecher Pairs with Adjustable Bridges].— Elektroswias, Leningrad, p. 158.
 Tests on Stranded Wires.—List, p. 160.
 A Three-Sided Radio Tower [Self-Supporting 200-Foot Tower, Steel Tube Construction].—Couzin, p. 101.
 A 207-Metre Tower as Radio Aerial, p. 273.
 Notes and Recollections on the Erecting of the Towers of the Wireless Station of Croix d'Hins [near Bordeaux : Metal Tripods 250 Metres High, and Their Foundations].—Pomey, p. 40.
 Wooden Towers at the Leipzig Broadcasting Station.—Herbst, n. 160.
- p. 160. The Effect of Metal Towers on the Radiation from an Aerial [Eiffel
- Tower Diagram].—David, p. 160. A Proof that the Induction Motor Circle Diagram applies to the Transmission Line.—Creedy, p. 327. Transmission Lines for Short-Wave Radio Systems.—Feldman,
- p. 160.
- Graphical Methods for Problems involving Radio-Frequency
- Graphical Methods for Problems involving Radio-Frequency Transmission Lines.—Roder, p. 327. A Simple Method of Measuring the Attenuation of Transmission Lines [H.F. Feeders, etc.].—Strutt, p. 327 (two). Transmission Lines : see also Feeders, Lecher Wires. Checking the Behaviour of Ultra-High-Frequency [2. and 5-Metre] Waves : Interesting Transmission Tests using Directive Aerials [Wave Reflectors and Directors].—Jones, p. 328. Feeders for Ultra-Short Waves.—Bahnemann, p. 159. A Study of [Ultra-] Short-Wave Directive Antennae.—Chiba, Taki and Ito, p. 101. Absorption and Reradiation of [Ultra-] Short Electric Waves.— Fountain, p. 327.

- Absorption and Reradiation of [Ultra-] Short Electric Waves.— Fountain, p. 327. Special Aerials for the Transmission and Reception of Ultra-Short (80 cm) Waves.—Morita, p. 159. Some Notes on "Wave Canal" [Directional Aerial System for Ultra-Short Waves, using a Line of Wave Directors with Metallic Plates forming a Partial or Complete Rectangular Tube].— Nakamura, p. 505. The Pickard Dipole System for Ultra-Short Waves, using Untuned Feeder with Special Coupling Transformer.—Pickard, p. 567. Aerial and Reflector System for Ultra-Short Waves.—RCA, p. 273. Reflectors for Ultra-Short Waves.—Telefunken, p. 449.

- Aerial and Reflector System for Ultra-Short Waves.—RCA, p. 273.
 Reflectors for Ultra-Short Waves.—RCA, p. 273.
 Reflectors for Ultra-Short Waves.—RCA, p. 273.
 Reflectors and Ultra-High : see also Matching.
 A Variable Wavelength Aerial [Aerial Wire winding on Metal Drum: Improved Short-Wave Reception by Adjusting to Optimum Natural Wavelength], p. 567.
 The Radiation Characteristics of a Vertical Half-Wave Antenna.—Stratton and Chinn, p. 214.
 Vibration in Electrical Conductors [and the Advantage of a Triangular Cross Section].—Davison, Ingles and Martinoff, p. 40.
 A Vibration-Damping Lever for Attachment to Overhead Lines near Point of Suspension.—Schmitt, p. 215.
 Conductor Vibration from Wind and Sleet.—den Hartog, p. 394.
 Mechanical vibrations in Transmission Lines.—Niven, p. 273.
 Theoretical and Experimental Investigations of the Vibrations in Overhead Lines.—Schmitt and Behrens, p. 506.
 Measurements of Wind Pressure on Overhead Wires.—Sherlock, p. 40.

- p. 40.

VALVES AND THERMIONICS

The Dependence of Adsorbed Ions on Temperature .- Becker and

- Ine Dependence of Adsorbed lons on remperature, Decker and Brattain, p. 508.
 American Papers on New Valve Types : see below.
 New Amplifiers, Detectors and Rectifiers [Multifilamentary Cathodes : Electron Coupling : Class B : Diode-Pentode, etc.], p. 273.
 Progress in Tubes for Radio [RCA Radiotron and Cunningham 2027; Dartifica, Davise, Darabian Carpida 9.4 with Multi
 - Progress in Tubes for Radio INCA realistication and Chammedian 25Z5 Rectifier, Power Amplifier Triode 2A3 with Multi-filamentary Cathode, etc.], p. 328.
 Developments in the Electrical Industry during 1932: Elec-tronic Tubes [including Improved Pliotron for Sensitive tronic Tubes [including Improved Pliotron for Sensitive
 - Developments in the Electrical Industry during 1932: Electronic Tubes [including Improved Pliotron for Sensitive Measurements at Low Frequencies, with Cathode between Grid and Anode], p. 328.
 Triple Grid Power Armplifier Tubes [as Suppressor Grid Output Pentode, Class B Zero Bias Output Valve, or Class A Low Impedance Triode].—Herold, p. 161.
 Radio Tube Progress [Arcturus 58: Radiotron 55—Two Diode and Triode Unit; Radiotron 82—Full Wave Rectifier]. p. 102.

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- Some Facts About the Recently-Announced Tubes [Types 41-44, 52, 55 and 85 (Duplex-Diode Triodes), 83 (Mercury-Vapour Rectifier), 89, Wunderlich and Triple-Twin], p. 41. Still More Tubes [including "Pentagrid Converters" and "Duo-Diodes" with Pentodes in Output Portion], p. 450. New Vacuum Tubes and Their Applications.--Hull, p. 328. "Characteristics of American Electronic Tubes: with Chart.---

- Characteristics of American Electronic Tubes : with Chart,---Henney, p. 102. Coefficient of Amplification of Triodes [Discussion of Chief Methods of Measurement].--Dei, p. 569. New Vacuum Valves and Their Applications [Special Pliotrons, Cathode-Ray Tube for X-Ray Chemical Analysis, Thyratrons, and Phanotrons.--Hull, p. 160.
- Observations of a Barium Cathode, sputtered on Nickel, with an Electron Microscope.—Brüche and Johannson, p. 569. New Valves at the Berlin Radio Exhibition : Binodes and 9-Watt
- Pentodes, p. 569. Thermal and Photoelectric Emission from Caesium-Caesium Oxide Cathodes, and the Influence Exerted on Emission by Inclusion
- of Caesium Atoms in the Dielectric.—de Boer and Teves, p. 507. Fine but Strong Low-Current Oxide-Coated Cathodes with Tungsten (Molybdenum, Tantalum) Core coated values with Augsten (Molybdenum, Tantalum) Core coated with Nickel (Platinum, Cobalt). p. 625. The Catkin Valve, p. 394 (three). Audio System with the New 2B6 Tube [for Class A Triode Output].—
- Stromeyer, p. 625. Special Two-System Valve for Class B Amplification.—Cossor Ltd.,
- p. 274. Class B Amplifiers considered from the Conventional Class A
- Standpoint.—Nelson, p. 506. Tubes with Cold Cathodes [Glow Discharge as Electron Source].—
- Hund, p. 215. Cold Cathodes : see also Corona, Filamentless, Glow Discharge. Surfaces from which Cold Emission Currents appear only at Very

- High Field Gradients.—Chambers, p. 451. Effect of High Series Resistance on Cold Emission.—Mebs, p. 507. Electronic Emission from Cold Metals.—Henderson, p. 274. Note on Contact Potential Difference [and Thermionic Work Func-tions].—Waterman, p. 508.
- Contact Potential Differences between Different Faces of Copper Single Crystals.—Farnsworth and Rose, p. 631. A Corona-Discharge "Valve" at Atmospheric Pressure.—Gemant,
- n. 394.
- Detector Tube Performance Curves [Diode; Conventional De-tectors; Duplex Diode-Triodes; Types 75 and 2A6, with High-Mu Triode Section; Duplex Triode Pentodes].—Nelson,

- High-Mu Triode Section; Duplex Trode-remotes, Action, p. 450.
 The 77 as a [Self] Biased Detector with 100 Volts Plate Supply [for Small Universal A.C.-D.C. Receivers], p. 450.
 Considerations on Detector-Output Tube Systems [and the Possibilities of the Two-Valve Superheterodyne].—Nelson, p. 450.
 A New Type of Valve Diagram [showing "Durchgriff" Mutual, Conductance and Internal Resistance, and also "Güte",—Product of Mutual Conductance and Amplification Factor].—Gundlach, n. 41. lach, p. 41. A'New Type of Valve Diagram.—Howe: Gundlach, p. 161. Valve Data Diagrams : Correspondence.—Basto : Koga : G.W.O.H.,
- Valve Data Diagrams Content of Valves [Valve Diagrams including ..., 64].
 The Graphical Classification of Valves [Valve Diagrams including ..., Graphical Classification, p. 568.
 The Double Diode Triode.—Smyth and Stewart, p. 394.
 The Inner-Grid Dynatron and the Duo-Dynatron.—Hayasi, pp. 600 and ..., Hayasi, Pp. 600 and Pp. 600 and

- 620-621.
- 620-621.
 Testing the Elasticity of Vacuum Tube Filaments.—Marshall, p. 41.
 The Course of the Electrical Field in Electronic Valves, measured in the Electrolytic Trough.—Barkhausen and von Brück, p. 273.
 "Electrometer" Valves versus Ordinary Triodes in Valve Voltmeters with High Input Impedance.—McFarlane, p. 569.
 Electronics and Electron Tubes.—McArthur, pp. 395 and 506.
 Electronic Phenomen in Radioelectric Valves.—van Rough Crystalline Metal Surfaces.—Seemann, p. 161.

- Metal Surfaces.—Seemann, p. 161. The Spatial Distribution of the Emission from Incandescent Cathodes—Hamacher, p. 216.
- On the Secondary Emission from the Grid in Triodes [Experiments indicating an Emission due to Photoelectric Effect of Soft X-Rays from Cathode.]—Pinna, p. 161. The Variation of Secondary Emission with Heat Treatment.— Corocherd. 2005
- Copeland, p. 395. Copeland, p. 395. The Emission Valve Modulator for Superheterodynes [Four-Grid Detector Oscillator].—Wheeler, p. 328 : see also Hexode. The Radio Exhibitions in Paris 1932, [including Transmitting and
- The Radio Exhibitions in Parts 1932, including Transmitting and Receiving Valves], p. 506. Exponential Valves : see Screen-Grid. The Rôle of Vacuum Tubes in a Tube Factory.—Koechel, p. 451. The Valve Filament.—Beatty, p. 161. New Developments in Filamentless Tubes.—Hund, p. 274. Filamentless Radio Tubes Demonstrated for Wide Use.—Hund : Wired Radio, Inc., p. 328. The Filamentless Tube, p. 394.

Values and Thermionics.

- Filamentless: see also Cold Cathodes. Indirectly Heated Valves with Double-Wound [Non-Inductive] Filaments, p. 328.
- Method of Fixation of Emissive Material on Cathode Tubes heated by Internal Filament.—Lévy, p. 329. The Flash-Arc ["Rocky Point Effect"] in High-Power Valves.—
- Gossing, p. 41. Electric Currents from Hot Cathodes in Gases and Vapours at Atmospheric Pressure.—Ruhnke, p. 41. Valve with Glow Discharge as Electron Source.—Telefunken,
- p. 102.
- Non-thermionic [Glow Discharge] Amplifier Tube .--- Reich, А p. 161.
- Application of Graphite as an Anode Material to High-Vacuum
- Application of oraginite as an Anode Material to Figh-Vacuum Transmitting Tubes.—Spitzer, pp. 451 and 569. Investigations on the Setting-In Point of Grid Current in Amplifier Valves [Comparison between Directly and Indirectly Heated Cathodes].—Rothe, pp. 95-96. Grids for Tubes [Comparison between Molybdenum and Nickel].— Hunter a 109.
- Hunter, p. 102.
- The Heat of Evaporation of Electrons in the Thermionic Effect .----

- The Heat of Evaporation of Electrons in the Inermonic Effect.— Franzini, p. 395. Circuit for Determining Heating Time of Vacuum Tubes [using Telecron Clock].—Koechel, p. 102. The Hexode Vacuum Tube: Emission-Valve Mechanism.— Wheeler, p. 450 (two). The Hexode, a new German Valve.—Wigand: Telefunken, p. 450. Hexodes, a New Type of Receiving Valve.—Telefunken Company, p. 506 p. 506.

- Hexodes: see also Emission Valve, Superheterodyne.
 Rectifiers and Oscillators with 220-Volt Valves, and Tests on High-Voltage Rectifier Valves.—Diefenbach: Hartel, p. 625.
 A "Low-Hum" Vacuum Tube [No. 262A High-Gain A.F. Amplifier for A.C. Mains].—J. O. McNally: Western Electric Company, p. 215.
- A Study of Hum Generation in Vacuum Tubes as affected by Heater Design.—Glauber and Campbell, p. 569.
 I.E.E. Wireless Section : Chairman's Address. Part I : Thermionic Valves. Part II : Spontaneous Fluctuations in Valve Amplifiers. —Turner, p. 215.
- -- Jurner, p. 215. Imported Valves.--Application for Marking Order under the Mer-chandise Act, p. 506. On the Density Distribution of Unipolar Ion Currents [Theoretical Investigation].--Deutsch, p. 330. A Life-Test Power Supply utilising Thyratron Rectifiers.--Lord,
- p. 570.
- p. 570.
 The Behaviour of an Electronic Valve with a Ferromagnetic Anode in a Magnetic Field.—Schwarzenbach, p. 624.
 On the Influence of the Magnetic Field of Filament Currents on the Electron Path.—Hamacher, p. 273.
 Various Papers and Patents on Magnetron Oscillators, p. 624.
 Magnetron : see also Ultra-Short.
 Dynamic Measurement of Electron Tube Coefficients.—Tuttle, p. 506.

- p. DUD. Dynamic Tube Measurements over Wide Ranges of Values [by Valve Bridge].—Tuttle: General Radio, p. 102. Grid and Plate Currents in a Grid-Controlled Mercury Vapour Tube.—Seletzky and Shevki, p. 329. Emission of Metallic Ions from Oxide Surfaces. I,—Identification of the Ions by Mobility Measurements: II.—Mechanism of the Emission.—Brata: Powell and Brata, p. 625. "Sprayed Mica" used in Valves to prevent Leakage.—Na. U. Rad. Corp.; p. 329.

- Sprayed Miea, "used in Valves to prevent Leakage.—Na. U. Rad. Corp.; p. 329.
 Anti-Microphonic Valves ["Rigid Unit" Construction].—Mullard Company, p. 41.
 Measuring Microphonic Noise in Vacuum Tubes [Equipment in which Microphonic Response is indicated by Steady Deflection of Output Meter].—Pidgeon, p. 161.
 A Measuring System for Microphonic Noise Currents.—Kelley, p. 560.
- p. 569.

- D. Micropyrometry.—Lewin, p. 41.
 The Thermionic and Photoelectric Work Functions of Molybdenum. —Du Bridge and Roehr, p. 41.
 The [Experimental] Effect of High Electrostatic Fields upon the Vaporisation of Molybdenum [in the form of Heated Wires].— Estabrook, p. 330.
- Secondary Emission of Electrons from Molybdenum.-Copeland, p. 569.

- p. 569.
 The Effect of Temperature on the Emission of Electron Field Currents from Molybdenum and Tungsten.—Ahearn, p. 507.
 The Place of Nickel in Radio Tube Manufacture.—Marino, p. 215.
 Noise [Thermal and Shoi Effect] as a Limiting Factor in Amplifier Design.—Keall, p. 631.
 Inter-Carrier Noise Suppression : a New System [using the Wunder-lich B Valve with Additional Anode for Amplifying the AVC Potentials].—Wunderlich, p. 213.
 Non-Linear Valve Characteristics : a Brief Discussion on Their Use.—Bull, p. 216.
 Out-Gassing Electrodes by means of a Short Induction Winding moved to-and-fro in an Axial Direction.—Telefunken, p. 451.
- moved to-and-fro in an Axial Direction.-Telefunken, p. 451.

- The Output Power of the Final Valve in an Amplifier, and Its Practical Significance -- Kammerloher : Leithäuser, 45 DD. and 398.
- Amplifiers [Rapid Test Method].—Whitehead : Brain, p. 215. Emission from Oxide-Coated Cathodes.—Benjamin and Rooksby,

- Papers on the Investigation of Oxide Cathodes by means of the Electron Microscope.—Brüche and Johannson, p. 102. The Total Radiation from Oxide Cathodes.—Clausing and Ludwig,
- p. 625.
- Determination of the Work Function of [Barium] Oxide Cathodes.
- Heinze, p. 216. Phenomena in Oxide Cathodes, and Their Transverse Resistance.-
- Kroczek, p. 330. The Work Functions of the Components of Activated Oxide-Coated Cathodes.—Rentschler, Henry and Smith, p. 161. Oxide Cathodes : see also Barium. Caesium, Cathodes, Thoriated,
- Thorium.
- The Pentagrid Converter [Combined Oscillator-Detector for Super-heterodyne Receivers].—Lyons, pp. 394 and 564. A Power Amplifier Pentode Tube [Radiotron 48, Curningham C-48,]
- p. 102. On the Use of the Pentode Valve for Pressure Recording [in Fluids,
- using Capacity-Change Method : Pentode acting both as Oscil-lator and Valve Voltmeter by Suitable Use of the Three Grids].----

- lator and Valve Voltmeter by Suitable Use of the Three Grids].---Oliphant, p. 161.
 The Screened H.F. Pentode.--Goldup, p. 274.
 High-Frequency Pentodes.--Wigand, p. 506.
 Pentodes: see also Screen-Grid.
 The Emission from Glowing Platinum in Gases, in particular in Iodine Vapour and Chlorine.--Muller, p. 41.
 Thermionic and Adsorption Characteristics of Platinum on Tangsten.--Sears and Becker, p. 507.
 Vacuum Tube Characteristics in the Positive Grid Region by an Oscillographic Method.--Kozanowski and Mouromtseff, pp. 450 and 569.
 Fifeet of Aumonia on Positive Ion Emissivity of Iron, Nickel, and

- 450 and 569. Effect of Ammonia on Positive Ion Emissivity of Iron, Nickel, and Platinum.—Brewer, p. 395. The Emission of Positive Ions from Heated Metals : The Tem-perature Variation of the Positive Ions from Molybdenum.— Barnes, p. 161. Liberation of Electrons from a Metal under Bombardment by Slow Positive Icns [and Calculation of Minimum Potential Drop (of the order of 1 Volt) for which an Ion will extract Electrons].— Valle n. 395
- the order of two, as a second second
- [by a Modified Wheatstone Bridge Method].—Babits and Szalontay, p. 625. The Screen-Grid Valve as a Frequency-Changer in the Super-Het.—
- White, p. 99. The Behaviour of Screen-Grid Valves in the Presence of Secondary Electrons.—Herweg and Ulbricht, p. 506.
- The Internal Resistance of Screen-Grid Valves .- de la Sablonière, p. 507.
- p. 507.
 Secondary Emission in Thermionic, particularly Screen-Grid Valves [with Special Reference to H.F. Transmitting Valves].— de la Sablonière, p. 507.
 The Measurement of the Screen-Grid Loss of a Driven S.G. Transmitting Valve.—de la Sablonière, p. 507.
 Screen-Grid, Pentode and Exponential Valves.—Heinze, p. 625.
 Papers on Shot Effect and Thermal Agitation, and the Initial and Final Amplitudes of a Damped Oscillatory Process.—Barkhausen and Höseler, n. 625.

- and Hässler: Hässler, p. 625. Radio Tubes in Need of Simplification.—Bureau of Standards, p. 329.
- Valves for Sound Picture Systems.—Kelley, p. 569. Space-Charge Currents at High [and Ultra-High] Frequencies.-
- Protze, p. 568. Space-Charge Phenomena in Electronic Valves [and the Anomalies in the Static Characteristic of the Hull Magnetron] --- Schwarzen-
- bach, p. 624. Thermionic Tubes in which Grid- and Anode-Sections, in Plane perpendicular to Cathode, form Spirals one within the other,
- p. 274. The **Spray Shield** Tube.—Parker and Fox, p. 394. The New Valves [Mixing Hexode, Fading Hexode, and Binode] and Their Connections in Superheterodyne Receivers.—von der

- and Their Connections in Supermeteroughe Receivers.—von der Bey, p. 625. Vacuum Tubes [Survey for 1932].—Davies, p. 215. Valves [a Survey of Ten Years].—Ponte, p. 329. New Material for Radio Tubes ["Svea" Plate and Wire for Elec-trodes, Plates, Getter Cups, Screens, Lead-in and Support Wires, etc.].—Todd, p. 102.

Valves and Thermionics

New Tubes : New Tube Materials [particularly Svea Metal], p. 451 New Telefunken Valves [and in particular the Biflar Cathode].— Schröter, p. 625. See also Transmitting. Theory of Thermionic Vacuum Tubes.—Chaffee (Book Review),

- p. 506. Thermal Agitation of Electrons in a Metallic Conductor [Verification of Nyquist's Theory, and Precision Measurement of Boltzmann's Constant].—Williams and Wilbur, p. 161.
- The Thermionic Effect treated according to the Fermi Statistics and Wave Mechanics.—Rossi, p. 102. The Deactivation—Dispersion of the Thorium Layer—of Thoriated
- Tungsten through Bombardment by Positive Ions [Contra-diction of Kingdon and Langmuir's Theory].—Gehrts, p. 329. The Processing of Thoriated Tungsten Filaments.—Ausman, p. 569.
- The Diffusion of **Thorium in Tungsten** [and the Effect of Size of Grain].—Fonda, Young and Walker, p. 330. Thermionic and Adsorption Characteristics of **Thorium on Tungsten**.
- -Brattain and Becker, p. 330. Characteristics and Functions of Thyratrons.—Hull, p. 339. Radiation-Cooled Power Tubes for Radio Transmitters [with Peak Output Capacities 500, 1 500, and 2 000 Watts].—Mendenhall,
- On Short Wave Transmitting Valves [and the Superiority of the Low-Voltage High-Emission Type].—Haraguchi, p. 41. Telefunken Transmitting Valves [including Short- and Ultra-Short-Wave Types, and Special Valves for Decimetre Waves].—Kühle, p. 101 p. 101.
- 300 kw Transmitting Valve for Hilversum .- Philips Company,
- 900 kw transmitting varie for finitestant ramps completely p. 624. [German] High-Power Transmitting Valves, p. 624. Present and Possible Future Trends in Radio [including Steel for Valve Anodes, etc.], p. 326. A Theory of Available Output and Optimum Operating Conditions
- A Theory of Avanable Output and Optimum Opticing Conductors for Triode Valves,—Callendar, p. 568. The Dial-Coded Universal Tube Checker and Circuit Analyser.— De Soto, p. 506. The Emission of Positive Ions from Hot Tungsten.—Moon, p. 41. The Potential Difference between Incandescent Tungsten Electrodes

- at Different Temperatures.—Kuhn, p. 161. The Positive Ion Work Function of Tungsten for the Alkali Metals.

- -Evans, p. 330. —Evans, p. 330. New Tube Type Designations [Valve-Numbering System adopted by American Radio Manufacturers Association], p. 450. Tube Types Tabulated [including Sections for Special Types and for Western Electric Transmitting Tubes], p. 41. The Indirectly-Heated Triode as Generator of Ultra-Short [Micro-]
- Waves.—Giacomini, p. 501.
 Measurements on Valves for Generating Ultra-Short Waves [Micro-Waves down to 5 cm : including a Special Duplex Valve].—
- Waves down to 5 cm: including a Special Duplex Valve].— Gossel, p 567.
 Magnetostatic Oscillators for Generation of Ultra-Short Waves.— Rilgore, p. 154.
 Valves for Ultra-Short Waves: Reduction of Inductance of Grid Electrodes by Combination of Two or More Helices in Opposed Sense.—Kohl, p. 450.
 Valves for Ultra-Short Waves: Preventing Deformation of Grid Electrode by Insulating Strip made fast to Nodal Points of Spiral.—Kohl, p. 450.
 The Magnetron Ultra-Short-Wave Oscillator.—Megaw, p. 329.
 The Design of Triodes for Ultra-Short [Electron Oscillation] Waves. --Morita, p. 161.

- Ine Magnetron Ultra-Short-Wave Oscillator.—Megaw, p. 329.
 The Design of Triodes for Ultra-Short [Electron Oscillation] Waves. —Morita, p. 161.
 New Forms of [Ultra-] Short-Wave Tubes [including the "Standing Wave" and "Magnetostatic" Oscillators].—Mouromtseff, Kilgore and Noble, p. 98.
 Vacuum Tubes for Ulse at Extremely High Frequencies [Very Small Triodes and S.G. Valves for Ultra-Short (Micro-) Waves].— Thompson and Rose : Thompson, pp. 450 and 624.
 Ultra-Short : see also Magnetron, Space-Charge.
 On the Effect of High Electrostatic Fields on the Vaporisation of Metals [Theoretical Discussion].—Worthing, p. 330.
 The Westinghouse Industrial Tube DRJ-571, an Indirectly Heated Multi-Grid Valve giving Constant Current Output for Plate Potentials varying from 10 to 400 Volts.—Haller, p. 625.
 The Temperature Dependence of the Work Function for Composite Surfaces..—Brattain and Becker, p. 508.
 The Work Functions of Electrons Emitted from Metals.—Tamm and Blochinzev, p. 395.
 A New Method of Determining Thermionic Work Functions of Metals and Its Application to Nickel.—Fox and Bowie, p. 508.
 The Tenspection of Indirectly Heated Cathodes by X-Rays.—Dejardin and Directive Heated Cathodes by X-Rays.—Dejardin

- The Inspection of Indirectly Heated Cathodes by X-Rays.-Déjardin
- and Thovert, p. 161. Experiments of the Contact Potential of Zinc Crystals.—Zisman
- and Yamins, p. 330.

DIRECTIONAL WIRELESS

- A Note on the Theory of Night Errors in Adcock Direction-Finding Systems.—Coales, p. 42.
- The Cause and Elimination of Night Effects in Radio Range-Beacon Reception ["Transmission-Line" Aerial System : Application of Adcock Aerials to Equi-Signal Beacon).—Diamond, p. 162.

- Phase Synchronisation in Directive Antenna Arrays, with Par-ticular Application to the Radio Range Beacon [using the "Trans-mission Line" Antenna, Adocek Principle].—Kear, p. 625. Wireless Direction Finding [Marconi-Adocek Installations at Pulham and Lympne: another for Dubendorff].—Marconi Com-reguer, 231
- Pulham and Lympne : another for Dubendorff. Marcon Company, p. 331.
 Radio Aids to Air Navigation [New Target-Flight Radio Compass, and Its Combination with Magnetic Compass for Automatic Steering Control with Drift Correction : Landing Aids].—Green and Becker G.E.C., p. 395.
 Automatic Steering Control with Automatic Radio Drift Correction, for Aircraft.—G.E.C., p. 331.
 Radio System for Blind Landing of Aircraft.—Bureau of Standards, m. 45, 1508 and 570.

- Radio System for Bind Landing of Aircraft.—Bureau of Standards, pp. 451, 508 and 570.
 Radio System for Landing Aircraft during Fog: Installation at Newark Airport.—Diamond, p. 570.
 Blird Landing of Aircraft [A Survey].—Gloeckner, p. 162.
 Supersensitive Recorders of Altitude- and Temperature-Variations,
- for Aircraft.—Idaa, p. 102. Radio Guidance [for Aircraft, using Two Rotating Beacons trans-mitting Simultaneously on Same Frequency].—Miller, p. 162. Aircraft : see also Fog, and under "Atmospherics and Atmospheric
- Electricity
- The Automatic Communication to a Moving Craft of its Bearings taken by two Fixed Stations.—Csejkovits and Dieckmann, p. 451.
- Radioelectricity in Aviation [a Survey of Ten Years] .- Franck, p. 331.
- The Production of Two Horizontal Beams rotating in Opposite Directions, by feeding a Single Greek-Pattern Array at one End with a Periodically Varying Wavelength.—Longo, p. 508.
- Blind Landing : see Aircraft, Fog. Shipboard Observations with a Cathode-Ray Direction Finder between England and Australia.—Munro and Huxley, p. 41.
- The Gathode-Ray Direction Finder used for examining Long-Distance Short-Wave Signals.—Hollingworth, p. 102. Radio Direction Finding [including the Cathode-Ray Cyclograph].—
- Mesny, p. 396. Cathode-Ray Compass .--- Ende and Gloeckner : The A.E.G.,
- p. 570. Radio Compass developed in H.M. Signal School.—Horton and A
- Crampton, pp. 395 and 625. Direct-Reading Direction Finder with Continuously Rotating Gonometer Coupling Coil.—Dieckmann and Berndorfer, pp.
- 162 and 274. Direct-Reading Direction Finder.—I. T. and T., p. 274. A New Beacon for Irish Waters Lightship Automatic Wireless Beacon combined with Submarine Sound Transmitter, giving
- Beacon combined with Submarine Sound Transmitter, giving Distance as well as Bearing], p. 396. Distance Determination by Electromagnetic Waves.—Weigl, p. 451. Elimination of 180° Error in a Frame Aerial by the Use of the "Diffusion Coupling,"—Cordebas, p. 626. Errors in Direction-Finding Calibrations in Steel Ships due to the Shape and Orientation of the Aerial of the Transmitting Station. —Coales, pp. 395 and 625. Automatic Correction of Errors in Direction Finding.—Telefunken : Leib. n. 274
- Automatic Correction of Errors in Direction Finding. Felerunken: Leib, p. 274.
 An Inverter-Lamp for the Conversion of 60-Cycle Power into 1 0C0 Cycle Modulated Light (with particular Application to Modulated Light Beacons and Tuned Photoelectric Cell Receivers for Air-craft Direction in Fog]. —Westendorp, p. 42.
 Direction Signalling in Fog. —Della Riccia, p. 162.
 Sonic Marker Beacon for Fog Landing [Fan-Shaped Beams of 3000 c/c Whitel_ __Rice n. 331
- c/s Whistle].—Rice, p. 331. Fog Landing by Wireless [Newark Air Port], p. 626.

- Fog Landing by Wireless [Newark Air Port], p. 626.
 Fog : see also Aircraft.
 An Improved Goniometer-Type Direction Finder for High-Frequency Waves [using Adoock Aerials and a Divided Search Coil].—Tsukada, p. 102.
 The Precision attained by a Goniometric Frame, and the Convenience of the "Radio Line."—Bertin, p. 396.
 The Elimination of Night-Course Variations in Radio Range-Beacons [by Replacing the Crossed Loops by Two Vertical Towers, giving No Horizontally Polarised Components].—Kear, p. 274.
- Night Course, Effects, Errors ; see also Adcock, Polarisation, Ultra-Short.
- Short. On the Solution of the Problem of Night Effects with the Radio Range Beacon System [the "Transmission Line" Antenna System: Adcock Principle].—Diamond, p. 508. The Influences of the Earth's Magnetic Field on the Polarisation of Sky Waves [and Its Bearing on Errors in Direction-Finding]. —Baker and Green, pp. 385-386. The "Iron Ring Quotient Meter."—Geyger, p. 451. S.F.R. Transmitter for Radio Alignment ["SADOD" System], n 966

- S.F.K. Transmitter for Kadio Angininent [SADOD System], p. 626.
 A New Stroboscopic Direction Finder [for use on Moving Craft, particularly Aircraft].—Hardy, pp. 216 and 570.
 Transmission Line : see Adcock.
 Ultra-Short-Wave Beacons.—Kramar : Lorenz Company, p. 162.
 Ultra-Short-Wave Guiding Beam with Inter-locking Signals.—
- Telefunken : liberg, p. 274.

Directional Wireless.

- Ultra-Short-Wave Beacon [with Generating Circuit alternating between Positions on either Side of Focus of Parabolic Reflector]. —Telefunken: Ludenia, p. 451. A Radio Range Beacon Free from Night Effects [by the Use of Ultra-Short Waves].—Chinn, p. 508.

ACOUSTICS AND AUDIO-FREQUENCIES

- Effect of Position on the Absorption of Materials for the Case of a Cubical Room [and the Need of Caution in Applying the Usual Formulae for Absorption Coefficient and Decay Factor].--
- Formulae for Absorption Coefficient and Decay Factor].— Andree, p. 44. On the Most Favourable Space Absorption [and the Influence of the "Building-Up Period."]—Benecke, p. 333. The Theory of Sound Absorption in Porous Walls.—Cremer, p. 510. Measurement of the Acoustic Absorption Percentage at Oblique Incidence, with the Help of Standing Waves.—Cremer, p. 571. Absorption of Sound in Molecular Gases.—Kneser, p. 277 (two). The Effect of Humidity upon the Absorption of Sound in a Roon, and a Determination of the Coefficients of Absorption of Sound in Air.—Knudsen, p. 44. The Absorption of Sound in Air and Water Vapour.—Knudsen, n. 511.

- p. 511.
- p. 511. Absorption of Sound by Porous Materials.—Kühl and Meyer, p. 44. Workston of Acoustical Absorption Coefficients of Porous Bodies with the Angle of Incidence and the Frequency.—Kühl and Meyer, p. 572.
- The Absorption of Sound in the Atmosphere: a Suggested Ex-planation.—Rocard, p. 334. Fundamental Investigations on the Absorption of Sound.—Winter-
- Fundamental Investigations on the Absorption of Sound.—Wintergerst and Klupp, p. 219.
 A Measurement of the Fundamental Sound Generated by the Airscrew of an Acroplane in Flight: and The Propagation of Sound along the Slipstream of an Airscrew.—Paris, p. 511.
 Studies on the Sounds Emitted by Revolving Airscrews.—Obata, Yosida, and Morita, p. 277.
 Received Speech Amplifier for Telephone Subscribers.—Siemens & Halske, p. 218.
 The Subscriber Output Amplifier,—Winzheimer and Reppisch, n. 509.

- p. 509.

- p. 509. The Audio Transformer as a Selective Amplifier.—Pawley, p. 218. A High-Gain Audio-frequency Amplifier [using Screen-Grid Valves]. —Verman, p. 331. Supervisory and Control Equipment for Audio-frequency Amplifiers.
- -Sobort, p. 286. Graphical Determination of Performance of Push-Pull Audio Amplifiers.-Thompson, pp. 394-395. Filter-Type Interstage Amplifier Coupling.-Stone: Salisbury,

- Filter-Type Interstage Amplifier Coupling.—Stone: Salisbury, p. 628.
 The "Amplifilter" [applicable to Harmonic Telegraphy by Carrier Currents].—Kajii and Matsumae, p. 105.
 A New Acoustic Analyser.—Determination of the Sound Spectra produced by Aircraft in Flight [Microphone, Amplifier, and Tuned Bifilar Quadrant Electrometer].—Delsasso, p. 46.
 A Photoelectric-Mechanical Method for the Harmonic Analysis of Periodic Functions.—Dietsch and Fricke, p. 44.
 New Electrical Method of Frequency Analysis and Its Application to [the Detection and Measurement of] Frequency Modulation —Barrow, p. 45.
- -Barrow, p. 45. Analysis : see also Frequency, Harmonic, Measurement.

- Analysis: see also Frequency, Harmonic, Measurement.
 Developments in the Application of Articulation Testing.—Castner and Carter, p. 628.
 The Advantages and Disadvantages of the Articulation. Intelligibility, and Repetition Rate Techniques.—Collard, p. 452.
 Articulation : see also Intelligibility, Performance.
 Dynamic Microphones create New Requirements as to Noise Levels [Notes on the Design of Suitable Attenuators].—Bjorndal, p. 105.
 Audio System with the New 2B6 Tube.—Stromeyer, p. 625.
 A Theoretical Study on the Articulation and Optimum Reverberation of Auditoriums.—A. Hirayama, p. 163.
 Acoustics of Large Auditoriums..—Lifshitz, p. 219.
 Auditoriums is see also Enclosed, Room, Studio.
 "Automatic Secretary" for Recording Telephone Conversations without Electrical Connections to Telephone Circuit..—Loftin.-White Laboratories, p. 105.
 The Beat-Nole-Combinational-Tone Controversy.—Hazel and
- while Laboratories, p. 100. The Beat-Noie-Combinational-Tone Controversy.—Hazel and Ramsey, p. 623. Self-Biasing Output Circuit using Field Coil of Loud Speaker.— Thompson-Houston Company, p. 628. An Acoustic Illusion Telephonically Achieved [Binaural Recep-tion].—Fletcher p. 508

- An Acoustic fulligion felephonically Achieved [Binaural Reception].
 Binaural Reception.—Fletcher, p. 627.
 Binaural Sound-Locators.—Paris, p. 164.
 Success in obtaining Tonal Balance between Brass Band and Piano, Violin, etc., for Broadcasting.—Taylor Branson : Stokowski, p. 329. p. 332.
- p. 332.
 Average Energy Spectrum of a Broadcasting Station and Its Measurement.—Eckersley, p. 275.
 The Deadening of Sound and Vibration in High Buildings.— Genest, p. 452.
- Long Distance Telephone Circuits in Cable .-- Clark and Osborne, p. 46.

- Experimental Study on the Non-Loaded Cable used as a Long-Distance Telephone Line.—Matsumae, Yoshida, and Shinohara, p. 162.
- Calibration of Low Audio-Frequencies [using an Ordinary Electric-Calibration of Low Audio-Frequencies [using an Ordinary Electric-Mains Clock and the Output Stage of a Radio Receiver].— Meissner, p. 511.
 Vibrations produced in Bodies by Contact with Solid Carbon Dioxide [and Possible Applications].—Waller, p. 167.
 Carrier in Cable [and the use of a New Type of Amplifier embodying the Principle of "Negative Feedback"].—Clark and Kendall: Black, p. 628.
 Method of Recording Sound by means of a Cathode Ray.—von Hartel, p. 105.

- Hartel, p. 105.
- The Vibration Forms of Cone Diaphragms [Chladni Figures obtained
- by preventing the Powder from Sliding by Rotating the Cone about its Axis].—Benecke: Telefunken, p. 43. Papers on Chladni Plates.—Colwell, pp. 43, 219 (three), 275, and 452. Note concerning a Direct Reading Electrical Chronograph for Accurate Reading of Very Short Intervals of Time [for Echo Computing]. Direct Reading Lectrical Chronograph for Accurate Reading of Very Short Intervals of Time [for Echo
- Sounding).—Dubois and Laboureur, p. 164. Audio-frequency Constants of Circuits and Telephone Lines.— Chakravarti, p. 453.
- Preparations of Colloids by Supersonic Dispersion .- Marinesco,
- Preparations of Contours by Supersonal Englishing Correspondence,— Vibrations of a Coil-Driven Paper Cone : Correspondence,— Benecke : Pedersen : Strafford, p. 509. Natural Vibrations of a Conical Shell [Application to Loudspeaker

- Natural Vibrations of a Conical Shell [Application to Loudspeaker Theory].—Strutt, p. 627.
 Measurement of the [Frequency of] Radial Oscillations of Thin Aluminium Conical Surfaces.—van Urk and Hut, p. 627.
 The Resonance Frequencies of Two Coupled Oscillatory Circuits [and a New Method of Frequency Analysis and Non-Linear Distortion Measurement].—Fehr and Kreielsheimer, p. 562.
 Evaluating Hearing Aids [Determination of the "Figure of Merit" of any Device for Individual Cases of Deafness].—Harvey Fletcher, p. 167.
 Deeibel and Decineper Charts [for Simplifying Calculations of Transmission Lines and Amplifiers].—Sklar, p. 517.
 Delayed Speech [including the Magnetic Tape-Recording Method].—Hickman, p. 628.
- Hickman, p. 628.
- Acoustic Demonstration Experiment.—Waetzmann, p. 333. The Influence of an Air Cushion with Absorbing Back Wall on a Telephone Diaphragm.—Schuster and Hobberg, p. 275. The Axial Sound-Pressure due to Diaphragms with Nodal Lines.—

- McLachlan, p. 42. McLachlan, p. 42. Material for Experimental Diaphragms [Doped Tussore Silk].— Simeon, p. 165. Diaphragms: see also Cone, Discs, Loudspeaker, Propagation, Sphere, Vibrating. Office Dictating Machines need Better Fidelity, p. 105.

- Office Dictating Machines need Better Fidelity, p. 105.
 Perception of the Direction of Notes and Musical Sounds.—Reich and Behrens, p. 163.
 Directive Effect and Radiated Power of Acoustic Radiators and Radiator Groups in the Neighbourhood of a Reflecting Plane Surface.—Fischer, p. 219.
 The Acoustic and Inertia Pressure at any Point on a Vibrating Circular Disc.—McLachlan, p. 43.
 The Accession to Inertia of Flexible Discs Vibrating in a Fluid.—McLachlan, p. 42.

- The Accession to Inertia of Flexible Discs Vibrating in a Fluid.— McLachlan, p. 42.
 Distribution of Sound Radiation from Circular Discs with Nodal Lines [Mathematical Investigation].—McLachlan, p. 102.
 The Acoustic Power Radiated from Circular Discs with Nodal Lines [Mathematical Investigation].—McLachlan, p. 103.
 Dispersion of Sound in Several Gases, and Its Relation to the Frequency of Molecular Collisions.—Richards and Reid, p. 167.
 The Dispersion Theory of Sound.—Rutgers, p. 277.
 Remark on "The Dispersion Theory of Sound" by Rutgers.— Kneser, p. 272.
 Acoustic Method of Distance Measurement —Yagi and Matusuo, p. 572.

- p. 572.
- Permissible Amplitude Distortion of Speech in an Audio Reproducing
- Permissible Ampirtude Distortion of System.—Massa, p. 397. Amplitude Distortion compensated by Impedance decreasing with Amplitude Distorting Valve.—Massa, p. 571.
- p. 041. Interpreting Distortion Data.—Scroggie: Massa, p. 510. Requirements of Audio-Frequency Systems [including Tolerable Harmonic Distortion with Single-Sided and Push-Pull Con-nections].—Nason, p. 628.

- nections].—Nason, p. 628.
 Distortion in Recording and Reproduction of Sound [I. "Kinematic" Distortion, in Sound-on-Film and Magnetic Systems: Application to Secret Telephony].—Podliasky, p. 104.
 Ellipsoidal Functions and Their Application to Some Wave Problems. —Hanson, p. 580.
 An Acoustic Constant of Enclosed Spaces Correlatable with Their Apparent Liveness.—Albersheim and Maxfield, p. 276.
 The Fundamental Problem of Electro-Acoustics the Conditions for Fidelity of Reproduction of the Original Sound].—Koerts, p. 571.
 On the Fidelity of Reproduction of Sound.—Caporale and di Sabatino, p. 627. Sabatino, p. 627
- The Design of Filters for Carrier Programme Circuits .- Ralph, p. 452.

Acoustics and Audio-Frequencies

- Filters: see also under "Properties of Circuits," "Reception," and "Subsidiary Apparatus." The Theory of Acoustic Filtration in Solid Rods.--Lindsay and
- White, p. 219. Locating Fish by Submarine Echoes, p. 511. Note on Tyndal's Sensitive Flame.—Zahradniček, p. 276. Improved Burner for Singing Flames. Overtones in Vibrating

- p. 626.

- p. 620.
 Frequency Analysis : see also Analysis, Coupled.
 Automatic Logarithmic Recorder for Frequency Response Measurements.—Ballantine, p. 276.
 Papers on the Generation of Audio and Very Low Frequencies.— Mitra and Syam : Hueter, p. 36.
 An Improved Heterodyne Note Generator.—von Radinger, p. 398.
 Construction and Tests of Audio-frequency Generators.—Rosani, mp. 168 and 453
- Construction and Tests of Audio-frequency Generators.—Rosani, pp. 168 and 453.
 A New Type of L.F. Amplifier [Glow-Discharge Tube Coupling : for Frequencies from 0 to 10 000 c/s].—Schäfer : Peek, p. 212.
 The Shacktograph [a Portable, Mains-driven Gramophone with Electrical Reproduction, giving also Broadcast Reception and Home Recording], p. 165.
 The Evolution of the Gramophone.—Arbib, p. 275.
 [Gramophone] Amplifier Designs.—Dent, p. 276.
 Practical Experiences with the Home-Recording of Gramophone Discs.—Daudt, p. 627.
 Analysis of Sound Recording [on Gramophone Discs : Relations between Recording Technique, Playing Time, Loudness, etc.].— Hagemann, p. 627.

- between Recording Technique, Playing Time, Loudness, etc.j.— Hagemann, p. 627. The Modern A.C. Quality Amplifier [Self-contained Gramophone Equipment].—Page, p. 217. Home Recording of Gramophone Records.—Nesper, p. 44. Gramophone Tracking [a Geometrical Note].—Record, p. 44. [Gramophone] Turntable Design and Operation.—Gunsolley, p. 104. The Selenophon Sound-on-Strip Gramophones.—Rosen : Selenophon Compare n. 44.
- In e seienopnon Sound-on-Strip Gramophones.—Rosen : Seienophon Company, p. 44. Grid Current Compensation in Power Amplifiers.—Baggally, p. 217. Sub-Harmonics in Forced Oscillations in Dissipative Systems.— Pedersen, p. 628.
- A New Harmonic Analyser [Synchronous Disc and M.C.Voltmeter].
- -Gates, p. 218. Harmonic Content in Amplifiers [Indiscriminate Use of Power Basis

- Market, pp. 218 and 331.
 Modern Theory and New Experiments on the Acoustic Horn.— Bernini, p. 43.
 Sound Distribution from a Horn.—McLachlan, p. 217.
 The Theory of Horns [and some Experimental Investigations of the Validity of its Assumptions and Approximations].—Hall, p. 43. p. 43. The Hum due to the Sound-Reproducing Lamp in Sound-Film
- Equipments.—Kotowski, p. 509. The Determination of the Electroacoustic Parameters of a Telephone
- Receiver, and the Measurement of Acoustic Impedance [and of the Absorption Coefficients of Materials].—Sacerdote and Gotta,

- the Absorption Coefficients of Materials].—Sacerdote and Gotta, p. 187. The Design of Portable Speech Input Equipment for Remote Control Broadcasting.—Lyon, p. 105. Measurements of Sound Insulating Properties at Supersonic Fre-quencies.—Malov and Rschevkin, p. 44. Oscillographic Investigations on the Insulation, against Sound Transmission along Solid Bodies, provided by various Building Constructions.—Kreüger and Sager, p. 44. Loud Speaker requires Wider Band than Telephone Receiver for Equal Speech Intelligibility.—Lüschen : Hines, p. 102. The Influence of Side Tone upon the Intelligibility of Telephone Communication.—Pocock, p. 276. Intelligibility : see also Articulation, Performance. New Lamp for Sound-Recording and Television [Mercury Vapour, with Grid], p. 165.

- New Lamp for Sound-Recording and Television [Mercury Vapour, with Grid], p. 165.
 Recording a Foreign Language on to an Existing Film: the "Dubbing" Booths of the Jofa Studios, p. 105.
 The "Topoly" [Tobis-Polyphon] Process for Making Sound Films in Several Languages.—Neuburger, p. 43.
 Sound is Synchronised [the Use of the "Rhythmograph" in Transposing Sound Films into Other Languages].—Feinberg: Blum, p. 105.
 "Levels" in Electro-Acoustics [Suggestion of "Brigg" to replace TU, Decibel and Phon].—Vandeweile, p. 629.
 Dispersion of Light caused by Sound Waves [in a Fluid].—Debye, p. 167.
- p. 167.
- Some Experiments on the Diffraction of Light by Ultrasonic Waves [in Liquids].--Bär and Meyer, p. 453. Voice Transmission on a Beam of Light [Demonstration Apparatus].
- -Ramsey, p. 572. Electro-Acoustic Lissajous' Figures.—Carrière, p. 43. Judging the Loudness of Musical Sounds.—Trautwein, p. 105.

- An Experimental Determination of the Equivalent Loudness of Pure Tones.—Munson, p. 276. Estimating Loudness: Is the Ear an A.V.C. Device ?--Beatty,
- p. 332. Scales of Loudness.-Churcher and King, p. 452.

- Sches of Loudness,—Churcher and King, p. 492. Two Integral Laws of Acoustics. Loudness and Audibility Time of an Acoustic Impulse.—Lifschitz, p. 510. Loudness and Intensity Relations.—Ham and Parkinson, p. 43. Trends of Loud Speaker Design at the Paris Radio Exhibition : Comparison between Magnetic and Electrodynamic Types.— Otherway Jore Adam, p. 165.
- Loud Speaker with Composite Cone of Two or More Flexibly Con-nected Portions each Driven by its own Moving Coil.—AEG, p. 332.
- p. 302. Cone Loud Speaker with Cone Space taken up by Independent Filler [e.g., Wooden Cone] with Sound Channels leading to Flat Surface : to prevent Interference Effects due to Depth of Cone Diaphragm and to improve Frequency Characteristic.—AEG and Stenzel, p. 452.
- Measurements of Armature Forces in Loud Speakers .--- Amsel, p. 397.
- The be Electrodynamic Diaphragm Drive [for Moving-Coil Loud Speakers: the Optimum Mass for the Moving Coil].—Benecke, p. 42.
- Measurement of the Phase and Amplitude of Moving-Coil Loud
- p. 22.
 Measurement of the Phase and Amplitude of Moving-Coil Loud Speakers.—Binder, p. 216.
 Symmetrical Loud Speaker System with Soft Iron Laminated Field Magnets and Armature: Armature Flexibly Connected to Neutral Point of Field Magnet.—Noack: Borchardt, p. 332.
 Special Loud Speaker for Reproduction of Low Notes in Large Auditorium.—Charlin and Toulon, p. 103.
 Use of Cathode-Ray Oscillograph for obtaining Frequency-Response Curves [of Loud Speaker].—Davis, p. 570.
 How the Glow Loud Speaker].—Davis, p. 570.
 How the Glow Loud Speaker.—Gervin: Sawyer, p. 332.
 Theory of the Horn-Type Loud Speaker.—Hanna, p. 43.
 Some Accoustic and Telephone Measurements [British Post Office : including Loud Speaker Tests.—Harbottle, p. 43.
 Room Errors in Loud Speaker Tests.—Kellogg, p. 165.
 Electro-Acoustic Investigations on Electro-Magnetic Loud Speakers.

- Electro-Acoustic Investigations on Electro-Magnetic Loud Speakers.
- Electro-Acoustic Investigations on Lehmann, p. 331. Lehmann, p. 331. The Distribution of Sound Radiation from a Sphere vibrating in Various Ways: with Applications to Loud Speaker Diaphragms. McLachlan, p. 42. Sound Intensities: Volume Level and the Loud Speaker.—
- McLachlan, p. 43. Methods of Investigating the Vibrational Frequencies of Conical

- Methods of Investigating the Vibrational Frequencies of Conical Shells and Loud Speaker Diaphragms.—McLachlan, p. 103.
 Mathieu's Equation and the M.C. Loud Speaker [Analysis of Electro-Mechanical Rectification].—McLachlan, p. 103.
 Damping of Low-Frequency Oscillations in a M.C. Loud Speaker. —McLachlan, p. 103.
 Loud Speakers : Discussion at Informal Meeting of I.E.E.—McLachlan and others, p. 103.
 Loud Speakers : Discussion at Informal Meeting of I.E.E.—McLachlan and others, p. 103.
 Loud Speakers : Discussion at Informal Meeting of I.E.E.—McLachlan is Strutt, p. 331.
 On the Amplitude of Driven Loud Speaker Cones."
 —McLachlan, p. 509.
 Loud Speaker Performance and Design : Driving Mechanisms.—McLachlan, p. 627.
 A New Electro-Magnetic Loud Speaker Movement with Small Restoring Force when Field is Excited.—Nernst and Driescher, p. 397. p. 397.
- bord Speakers at the Berlin Show.—Nesper, p. 103.
 A New High Efficiency Loud Speaker of the Directional Baffle Type.—Olson, p. 43.
 A New Cone Loud Speaker for High Fidelity Sound Reproduction.
- -Olson, p. 452. The Field Coil of M.C. Loud Speaker used as L.F. Choke.-Olvensted,
- p. 165.
- Generation of Harmonics in Horn Loud Speakers : the Resulting

- p. 169.
 Generation of Harmonics in Horn Loud Speakers: the Resulting Power Limitation for these Instruments.—V. Rocard, p. 627.
 Reverberation and the Loud Speaker.—Sweeny, p. 165.
 Electrodynamic Loud Speaker of Speaken.—Sweeny, p. 165.
 Electrodynamic Loud Speaker of Speaken.—System, p. 165.
 Electrodynamic Loud Speaker of Speaken.—System, p. 165.
 Electrodynamic Loud Speaker of Speaker.—System, p. 165.
 Electrodynamic Loud Speaker of Speaker Diaphragms.— Telefunken : Gerdien and Neumann, p. 275.
 Hornless Large-Surface Loud Speaker dispensing with Baffle and Cabinet, Outer Edge of Diaphragm carried back to Wall of Room. —Teuke, p. 452.
 Loud Speaker with Large-Surface Membrane fixed at Edges and drawn out into Oblique Cone.—van Lier, p. 627.
 Loud Speaker: Curves and their Interpretation.—Voigt, p. 103.
 Further Investigations into the Acoustic-Electrical Transformation in Loud Speakers..—Zickendraht and Lehmann, p. 43.
 Electro-Acoustic Investigations on Loud Speaker.—Zickendraht and Lehmann, p. 43.
 Circuit for Disconnecting Loud Speaker Moving Coil from Amplifier when Field Excitation falls below a Limiting Value, p. 275.
 The Principle and Advantages of the "Free Swinging" Loud Speaker Movement, p. 43.

24

Acoustics and Audio-Frequencies.

- A New Moving-Coil Loud Speaker with Cone replaced by Flat Pleated Diaphragm, avoiding Air Column Resonance Effects, p. 43.
- Loud Speakers : see also Diaphragms, Discs, Horn, Propagation, Sphere, Vibrating. The Production of Homogeneous Magnetic Fields.—Bühl and
- Coeterier, p. 43. The Theory of Magnetic [Steel Wire or Band] Sound Recording.-Hormann, p. 104.
- The Magnetic Recording of Sound on Steel Bands.—Meyer and Schüller, p. 104. A Magnetostriction Oscillator producing Intense Audible Sound, and Some Effects obtained.—Gaines, p. 166. Match Your Impedances [and the Calculation of Audio-Transformer
- Ratios to Avoid Distortion].—Noble, p. 628. Real Power Matching and Apparent Power Matching [for Trans-mission of Max. Power from Source to Load].—Fischer, p. 34.
- Real Power matching and Apparent Power Matching [for Transmission of Max. Power from Source to Load].—Fischer, p. 34, Matching the Loud Speaker with the Output Stage.—Keller, p. 217. Pointer Instruments for Beat-Note Methods of Measurement [including Harmonic Analysis].—Laible, p. 110. The Absolute Measurement of the Fundamental Magnitudes in Acoustics.—Carrière, p. 333.
- Objective Measurements of Sound Intensity [Survey] .-- Trendelenburg, p. 510. The Objective Measurement of Sounds.—Trendelenburg, p. 628.

- The Objective Measurement of Sounds.—Trendelenburg, p. 628.
 Measurements and Tests Special to Telephony.—Cohen, p. 398.
 Acoustic Measuring Instruments for Practical Use.—Jaekel: Siemens & Halske, p. 218.
 Acoustic Measuring Instruments.—Hanson, p. 276.
 The Measurement of Mechanical Impedance to L.F. Alternating Torsional Motion: and The Recording of the Characteristic of a Mechanical Filter.—Paolini, p. 627.
 The Measurement of Mechanical Resistances to Rotary Motion [and an Electrical Method of producing Mechanical Resistances of Any Desired Value and Kind].—Paolini, p. 570.

- of Any Desired Value and Kind] —Paolini, p. 570. A Compensation Microphone of Very Small Dimensions [for Sound Field Measurements].—Geficken, pp. 217 and 333. Deflexions and Vibrations of a Circular Elastic Plate under Tension [Mathematical Investigation for application to Design of Con-denser Microphone].—Bickley, p. 333. A Miniature Condenser Transmitter [Microphone] for Sound-Field Measurements.—Hall, p. 103. A Pistonphone for the Determination of the Low-Frequency Response of the Condenser Microphone.—Obata and Yosida, p. 186.

- Response of the Congenerate Antopartical Construction of Two **y**-166. Velocity [Ribbon] Microphones: Practical Construction of Two Types That Are Easy to Make.—Melotte: Elliot, p. 217. The Ribbon Microphone [Theory].—Olson, p. 44. On the Collection of Sound in Reverberant Rooms, with Special Reference to the Application of the Ribbon Microphone.—Olson, 907
- New Velocity ["Ribbon"] Microphone Promises Revolutionary Broadcast Advances [Uniform Response from Zero to 14 000 Cycles/Sec].—RCA Victor, p. 103. The Ribbon Microphone and Its Applications.—Weinberger, p. 103.
- The Ribbon Microphone and Its Applications.—Weinberger, p. 103. The Advantages of the Light-Weight Crystal Microphone for Sound Picture Recording, p. 452. The Evolution and Present Condition of Microphone Technique.—
- Chavasse, p. 217. Some Remarks on the Classification of Microphones.—Charke-witsch: Schuster, p. 509. A Microphone Amplifier with Automatic Volume Control.—Berto-lettic, also
- lotti, p. 165.
- Microphone and Studio Technique, p. 628. Microphones : see also Flames. Quantitative Investigation of the Acoustic "Pull-In" [Mitnahme] Effect.—Chaikin, p. 45. Mized Circuits [for Combining Programme Elements on Several Channels], p. 628.
- A Machine which generates a Modulated Frequency Band .-- Dornig, p. 511.

- P. Statute and generates a modulater requency band Doring, p. 511.
 Modulation Products in a Power Law Modulator. Tynan, p. 621.
 Music Transmission over Short-Wave Commercial Radio-Telephone Circuits.—Gracie, p. 404.
 Perfect Quality and Auditory Perspective in the Transmission and Reproduction of Music. Jewett, p. 396.
 The State of Music. Jewett, p. 396.
 The State of Music. Stokowski's Orchestra in 16000-Cycle Fidelity at Ten-fold Volume, p. 452.
 The Scale of Sound Amplitudes in Musical Intervals.—Goodfellow, p. 510.
 The Society for Electrical Musical Intervals.—Goodfellow, p. 510.
 The Society for Electrical Musical Intervals.—Goodfellow, p. 510.
 The Society for Electrical Musical Intervals.—Goodfellow, p. 510.
 The Society for Electronic Musical Intervals.—Bunting, p. 165.
- p. 165. New Electronic Musical Instrument [Photoelectric Control of Neon
- Lamp Circuit.—Saraga, p. 165. Electro-Mechanical Oscillator particularly applicable to Electrical Musical Instruments.—Michaud, p. 452.

- Electronic Musical Instruments of Europe and U.S.-Miessner, p. 332.
- Electrical Musical Instruments, Their Methods of Action and Functions.—Janovsky, p. 627. Electrical Musical Instruments at the Berlin Radio Exhibition :

- Electrical Musical Instruments at the Berlin Radio Exhibition -Editorial, p. 44.
 Electrical Musical Instruments: see also Organ, Piano, Trautonium.
 The Loudness of Noises [a New Theory and the Failure of the Old]. —Barkhausen and Steudel, p. 510.
 The Radio-Noise Meter and Its Application to the Measurement of Radio Interference.—Barhydt, p. 392.
 A Study of Noises, and of the Accoustic Insulation of Materials and Buildings.—Cellerier, p. 46.
 Summation Methods in Noise Problems.—Churcher, King and Davies. n. 628. Davies, p. 628.
- The Frequency Analysis of Aircraft Noises [using the Exploring Note Method and The Rectifier Bridge Analyser] —Eisner, Rehm
- Noise Method and The Rectifier Bridge Analyser].—Eisner, Renm and Schuchmann, p. 48. Noise Measurement [Survey].—Free, p. 628. Researches and Measurements on Noise in the U.S.A. [including the Analyser and Its "Mechanical Filter"].—Hanna, Marvin and Wolf, p. 167. The Suppression of Noise [British Association Paper].—Kaye,
- p. 398.
- p. 595. Special Noise Testing Equipment.—MacNee, p. 276. Noise Measurements on Motor Vehicles.—Meyer and Willms, p. 46. The Barkhausen Effect as Noise Standard.—Nukiyama and Saito, p. 46.
- On the Accuracy of the Aural Method of Measuring Noises. Obata and Morita, p. 218. Practical Methods of Combating Noise in Industrial Works [General

- Account].—Osswald, p. 46. The Significance of Noise Mcasurements.—Pratt, p. 46. A Recording Noise-Level Meter: the "Pegelschreiber" and its Use by the German P.O.—Ribbeck and Wiedemann, p. 628.
- The Perception and Measurement of the Loudness [of Noises and Musical Notes].—Steudel, p. 510. The Noise Problem from the Standpoint of the Engineer.—Wagner,
- p. 217. A Note on Nonlinearity in Transducers used in Communication.
- -Caporale, p. 563. Measurements of Amplitude and Phase of the Octave in a Tuning
- Measurements of Amplitude and Phase of the Octave in a Tuning Fork.—Derjaguin, p. 572. The Coupleux-Givelet Electronic Organ.—Givelet, p. 165. Sound Ornaments.—Gradenitz: Fischinger, p. 332. A New Beat-Frequency Oscillator.—Bagno, p. 105. A New Mains-Operated Audio-Frequency Oscillator.—Brookes-Smith, p. 572.

- Low-Frequency Oscillator [delivering 23 Milliamperes into a 600 Ohm Load at Frequencies between 10 and 800 Cycles/Sec.].-A
- Hudack, p. 45. A Heterodyne Oscillator of Wide Frequency Range.—Kreer, p. 166. Beat-Frequency Oscillator Control : Determining the Proper Plate
- Shape.—Lampkin, p. 166. Standard Audio-Frequency Oscillator.—Standard Telephones &

- Standard Audio-Frequency Oscillator.—Standard Telephones & Cables, p. 511.
 Resistance-Stabilised [Audio] Oscillators [and Their Design Principles].—Terman, p. 688.
 Measurement of the Power Output of Low Frequency Final Stage Amplifiers.—Babits, p. 45.
 A Theory of Available Output and Optimum Operating Conditions for Triode Valves.—Callendar, p. 568.
 Detectors as Output Valves giving 800 mw : Power Grid Detection with High-Impedance Choke in place of Grid Leak.—de Cola.
- etectors as **Output** Valves giving 800 mw : Power Grid Detection with High-Impedance Choke in place of Grid Leak.—de Cola,
- with fight-impedance when the final Valve in an Amplifier, and Its practical Significance.—Leithäuser pp.45 and 398. The Maximum Power Outputs of Amplifier Valves, for Complex Loads [and the Optimum Matching Conditions].—Söchting, 185
- Maximum Output, Efficiency, and Optimum External Resistance of Output Valves [for Class A and Class B Amplification].--
- Output valves for class if and class in Low Frequency Amplifiers [Rapid Test Method] Whitehead : Brain, p. 215. A New Criterion of Circuit Performance [New Performance "Unit"]
- -Collard, p. 452.
- The Production of Specified Wave Forms with the Photoelectric Siren.—Knauss, p. 333. Determination of Working Characteristics at Different Frequencies,
- by the use of a Photoelectric Siren .- Schäffer and Lubszynsky, p. 45. A New System of Reproducing Sound Photo-Electrically.—Selgas
- and Laffon, p. 105. itroduction to the Photographic Recording of Sound.—Eggert
- and Laiton, p. 105. Introduction to the Photographic Recording of Sound.—Eggert and Schmidt, p. 332. A New Method of Sound-Pulse Photography [Foley Sound-Shadow Method modified to use Induction Coil in place of Electrostatic Machine].—Kalyanaraman, p. 46. Keyboard and Loud Speaker [Neo-Bechstein Piano].—Raven-Uast p. 017
- Hart. p. 217. Scientific Piano for Radio City, p. 332.

- The Sound Output of a Grand Piano .- Lübcke and Wernicke,

- Acoustic Fige-up for Philadelphia Orchestra broadcasts.—max-field, p. 219. Pick-Up Resonance and Needle Scratch.—Stewart, p. 104. The Pick-Up and the Fidelity of Reproduction.—Varret, p. 103. Special Pick-Ups for the Low Amplification provided by the German "People's Receiver," p. 627. On the Determination of Some of the Elastic Constants of Rochelle
- Salt [Piezoelectric Resonators] by a Dynamical Method. n 508
- p. 508. A Piezelectric Resonator with Uniform Response over a Given Range of Frequencies [and Its Use as Electro-Optical Relay, Microphone, etc.].—Guerbilsky, p. 508. Experimental Investigations on the Piezoelectric and Dielectric Properties of Rochelle Salt [and the Design of a Piezoelectric Microphone].—Schwartz, p. 164. Some Observations on the Acoustic Field of Piezo-Quartz Crystals. Bücke p. 929.
- -Bücks, p. 333. Some Observations on Oscillating Piezo-Quartz Crystals and their Acoustic Field.-Bücks and Müller, p. 572. On the Propagation of Sound Waves in Thin Anisotropic Plates.-
- On the Propagation of Sound Waves in Thin Anisotropic Plates,— v. Békésy, p. 167.
 The Propagation of Sound Waves of Finite Amplitude [Mathematical Analysis with Results applicable to High-Power Horn Loud Speakers],—Rocard, p. 216.
 Vast Public Address System at Thirty-First International Eucha-ristic Congress.—McPherson, p. 452.
 Quality in [Broadcast] Radjotelephony.—David, p. 218.
 Control of Sound Quality in Picture Production.—Deher, p. 217.
 Back to Quality in Radjo Receivers 1, p. 459.

- Countrol of Sound Quality in Picture Production.—Drener, p. 217. Back to Quality in Radio Receivers ! p. 452. Quasi-Standing Waves in a Dispersive Gas.—Bourgin, p. 220. Some Measurements on the Rayleigh Disc.—Kotowski, p. 45. On the Absolute Measurement of Sound Intensity by the Rayleigh Disc Method, and the Calibration of Microphones [Advantages of the Very Small " Piczophone '].—Niva and Nishimura, p. 166. Sensitive Rayleigh Discs for Acoustic Measurements.—Grösser, p. 453
- p. 453. Problem relating to the Theory of the Rayleigh Disc.-Kotani,
- p. 572

- p. 572. Acoustic Receivers.—Perrin, p. 333. The Voltage-Substitution Method of Determining the Sensitivity of Electro-Acoustic Receivers.—Lucder and Spenke, p. 332. Sound Recording for the Amateur.—Slade, p. 44. A New System of Sound Recording [Vertical Cut].—Harrison, p. 44. Recent Fundamental Advances in Mechanical Sound Records on Wax Discs using Vertical Cut. Demonstration.—Frederick, p. 975.

- Wax Discs using Vertical Cut. Demonstration.—Prederice, p. 275.
 Vertically Cut Sound Records.—Frederick and Harrison, p. 332.
 Measurement of the Reflecting Power of the Earth for Sound Waves at Normal Incidence.—Eisner and Krüger, p. 629.
 Reflection of a Sound Wave from a Circular Plate.—Sasao, p. 452.
 A New Method of Construction of a Sound Reflector giving Cylindrical Waves for Public Address Purposes].—Mulder, p. 163.
 The Acoustical Properties of Parabolic Reflectors [and a Comparison with Conical Horns].—Satô and Sasao, pp. 276 and 627.
 A Simple Resonance Receiver for Short Sound Waves.—Kröncke, p. 46.

- **Retarding Relay** for Synchronising Direct Reception and Loud Speaker Reception in Public Address Systems.—Gaumont, 217
- p. 217. A Modified Formula for Reverberation.—Millington, p. 219. A New Reverberation Formula.—Sette, p. 276. Reverberation Relations in Broadcast, Sound Film and Gramophone
- Reproduction.—Citron, p. 397. On Reverberation Time in Broadcasti, Sound Finii and Graniopholie Absorption by Artists themselves, etc.].—Hoshi, p. 510. Absolute Null Points of Sound Pressure produced by a Sinusoidal Sound Wave in a Room.—Hermann, p. 276. Combined Reverberation Time for Electrically Coupled Rooms.—
- Hill, p. 219. tudies on the Room Acoustics. Part I. Errata.—Hirayama,
- Studies p. 163. Model Tests on Room Acoustics and the Measurement of Acoustic
- Absorption Coefficients.—Khuner, p. 276. Resonance in Small Rooms.—Knudsen, p. 219. The Sound Field Distortions in the Neighbourhood of Absorbing

- p. 220. p. 220. On the Possibility of Determining the Slope of the Sea Bottom by means of a Single Acoustic Sounding.—Marti, p. 46. Acoustic Sounding Equipments, p. 46. Echo Sounding. XI.—Recent Forms of the British Admiralty Echo Sounder, p. 164.

- Corrections Applied to Echo Soundings, p. 164. The "Drive-In" Movie [Outdoor Automobile Sound-Film Theatre] p. 627.
- Sound Film Recording [especially the Photophone System] .-Federici, p. 105. The Damping of String Galvanometers for Sound Film and Re-
- cording Purposes. Soching : Selenophon Company, p. 165. The "Klarton" Sound-Film Process, with Special Attention to the Electro-Optical and Photographic Conditions.—Lichte and Narath, p. 275.
- The Breusing-von Hartel Sound Film Recording Process .--Rubert, p. 275.
- Sound Film Recording [particularly the RCA Photophone System].
- Sound Film Recording (Particularly the rest r instruments of the start particularly in the rest instruments of the start particularly in the rest instruments of the start particular particle recording. Sound Film: see also Photographic, Recording. Vacuum Tube and Photoelectric Tube Developments for Sound Picture Systems.—Kelley, p. 571.
- Acoustic Sourias.—Relievy, p. 371.
 Radio Acoustic Souria Ranging.—Rude, p. 164.
 Accession to Inertia of, and Power Radiated by, a Sphere Vibrating in Various Ways; with Applications to Hornless Loud Speakers. —McLachlan, p. 216.
- Stroboscopic Demonstration of Tones [Modification of Scripture's "Strobilion"].—Anderson and Lowery, p. 572. Acoustic Features of WCAU's New Studios [Philadelphia], p. 163.
- Acoustics of Broadcasting and Recording Studios (Enhance)may, p. 105. Acoustics of Broadcasting and Recording Studios.—Stanton and Schmid, p. 219. The Acoustic Problem in Broadcasting Studios [Convergent Walls, Stockholm and Malmö Studios, etc.].—Lemoine, p. 452. Studios : see also Auditorium, Enclosed, Room. Influence of Supersonic Waves on Chemical Processes.—Beuthe,
- p. 572.
- p. 572.
 Optical Method of Measuring the Absorption of Supersonic Waves by Liquids [based on the Diffraction of Light due to the Super-sonic Waves].—Biquard, p. 220.
 Supersonic Waves: Expressions for Energy Transmission and Decay of Amplitude with Distance due to Viscosity and Heat Conduction.—Biquard, p. 453.
 Unsuccessful Tests on the Transmission of a Supersonic Beam through Air.—Field, p. 453.
 Applications of Supersonics, including Depth Sounding and Sub-marine Signalling.—Florison and Vecchiacchi, p. 453.
 A Brief Survey of Supersonics.—Hubbard, p. 276.
 Experimental Methods for the Production and Study of Supersonic Vibrations. In "A Brief Survey of Supersonics."—Hubbard, p. 276.

- Vibrations. In "A Brief Survey of Supersonics."—Hubbard, p. 276.
 The Effect of Humidity on Supersonic Velocity in Air.—Kinoshita and Ishii, p. 276.
 Action of Supersonic Waves on Photographic Plates.—Marinesco and Trillat, p. 333.
 Experiments on the Absorption and Diffusion of Supersonic Energy.—Paolini, p. 166.
 Supersonic Dispersion and Absorption in CO₂.—Pielemeier, p. 44.
 Chemical and Biological Effects of Supersonic Radiation.—Szent-Györgvi, p. 277.
 Effect of Supersonic Vibrations on Unstable Systems.—Wood, p. 277.
 Heterodyne Detection of Supersonic Acoustic Waves in Air.—

- p. 277. Heterodyne Detection of Supersonic Acoustic Waves in Air.— Yagi and Matsuo, p. 511. The Restoration of Suppressed Speech Frequencies by means of a Non-Linearly Distorting Section.—Schmidt, pp. 398 and 628. Automatic Synchronisation of Tuning-Fork Oscillators by Lissajous Discrement Distorted Device 1, 499
- Automatic Synchronia and the of a function of the second o

- Massa, p. 397. Electrostatic Head Telephones.—Longo, p. 571. World-Wide Telephony—Its Problems and Future.—Gherardi and

- World wide Telephony—its Froblems and Future.—Onerata and Jewett, p. 46.
 The Thermophone and its Use as an Acoustic Measuring Instru-ment.—Geffcken and Keibs, p. 333.
 Thermophone : see also Threshold Values. II. The Thermophon and its Use as an Acoustic Threshold Values. II. The Thermophon and Keibs. p. 276.
- Determination of the Sound Pressure at the **Threshold** of Audibility by means of Thermophones.—Waetzmann and Geffcken, p. 333.
- p. 333.
 Absolute Measurements of the Loudness of Sound in the Region of the Threshold of Audibility.—Huizing, p. 510.
 A Note on the Theory and Practice of Tone-Correction.—Cole-brook, pp. 156 and 504.
 A Method of Tone Control.—Cope : Colebrook, p. 504.
 Output Decemperation Decimp.—Dent. p. 323.

- A method of Tone Control.—Cope : Colemony, 1, 304. Output Transformer Design.—Dent, p. 333. On the Audibility of Transient Phenomena, with Consideration of Space Acoustics.—von Békésy, p. 398. Amplification of Transients.—Smith, p. 509. A System of Effective Transmission Data for Rating Telephone Circuits.—McKown and Emling, p. 628.

A doustics and Audio-Frequencies.

Transmission of Sound through Partitions .- Davis, p. 219.

- The Trautonium.—Germann, p. 628. Determination of Velocity of Sound in Sea Water in Cape Cod Bay.
- -Cowie : Reed, p. 164. The Velocity of Sound in an Absorptive Gas.-Bourgin, p. 167. A Method for the Determination of the Velocity of Sound in Solids.
- -Richards, p. 219. The Velocity of Sound in Gases in Tubes.-Kaye and Sherratt,
- p. 511. Theory of Vibrating Membranes and Plates.-Colwell and Stewart,
- p. 43. The Transfer of Vibrational Energy between Molecules.—Kneser,
- p. 511.
- Vibrations of a Coil-Driven Paper Cone.--Strafford, p. 332.

- Vibrations of a Coil-Driven Paper Cone.—Strafford, p. 332. Vibrations in Solid Rods and Discs.—Field, p. 627. An Improved Vibrograph [for Analysis of Vibrations of Stretched Strings, Tuning Forks, etc.].—Tirunarayanachar, p. 167. A Thermionic Vollmeter with Logarithmic Calibration Curve [particularly for Electro-Acoustic Recording Equipments].— Rommel, p. 50. A Valve Voltmeter for Audio-Frequencies, Calibrated by Direct Current p. 511.

- A Valve Voltmeter for Audio-Frequencies, Calibrated by Direct Current, p. 511.
 Acoustically Compensated Volume Control for Radio and Phono-graph Sets.—Wolff and Cornell, p. 332.
 Volume Control by Potential Divider consisting of a Series of Mutually Decoupled Inductances each with the Same Time Constant as the Pick-Up.—Bethenod, p. 571.
 Fourier Analysis and Yowel Curves.—Nishet, p. 276.
 Fourier Analysis and Yowel Curves.—Scripture, p. 218.
 Observations on Filmed and Filtered Yowels.—Scripture, p. 44.

- Observations on Filmed and Filtered Vowels .- Benton : Paget, D. 44.
- p. 44.
 Researches on the Structure of the Vowels.—Kucharski, p. 276.
 On the Properties of Japanese Vowels and Consonants [Determination of the "Formanten" from Oscillograms].—Obata and Tesima, p. 572.
 Interference Elimination [in Reverberation Time Measurements] with the Warble Tone.—Barrow, p. 44.
 Weight as a Determining Factor in Sound Transmission.—Sabine, p. 9210.
- p. 219. The X-Ray Sound Film.- Grosse, p. 275.

PHOTOTELEGRAPHY AND TELEVISION

- Receiving Television in an Airplane.—Lubcke, pp. 108 and 167. Electron Diffraction and Photoelectric Effect at Alkali Metal Surfaces.—Kluge and Rupp. p. 455. High Frequency Amplification in Television.—Krawinkel and
- Ziebig, p. 47. The Calculation of a L.F. Amplifier for a Photoelectric Cell. Boutry, p. 221.

- Bolutry, p. 221.
 An Evacuated Amplifier Combination for the Measurement of Small Photoelectric Currents.—Custers, p. 384.
 A Method of Compensating the Plate Currents [in a Triode Amplifier applicable to Photoelectric Cells].—Donzelot and Divoux, p. 113.
 Marconi Television Amplifier with Flat Response Characteristics from 10 Cycles to 150 Kilocycles, p. 279.
 Field Strength and Ion Concentration near the Cathode of an Are Disobarge and Croct p. 279.
- "News" by Television : the Baird Process, p. 108. Five Years : the Development of the [Baird Television] Programmes,
- p. 279. The Theory of the Becquerel Effect [and the Distinction between It and the Hallwachs Effect and Photo-Conductivity].—Baur,
- Pook Reviews: Handbook of Phototelegraphy and Television: Photoelectric Cells and Their Use.—Schröter: Suhrmann, p. 108, Present Position of Technical Arrangements for Television Broad-
- casting.—Schriever, p. 630. Non-Loaded Cable for Picture Transmission, etc.—Matsumae, Yoshida, and Shinohara, p. 168. Collisions of the First and Second Kind in the Positive Column of a
- Caesium Discharge.—Mohler, p. 48. Thermal and Photoelectric Emission from Caesium-Caesium Oxide
- Cathodes and the Influence Exerted on Emission by Inclusion of Caesium Atoms in the Dielectric.—de Boer and Teves, p. 573. The Long-Wave Limit of Sensitivity of the Caesium-Oxide Photo-cell.—Widmer, p. 631. Characteristics of Certain Caesium-Oxide Photoelectric Cells.— Peters and Woodford, p. 47. The Spectral Sensitivity of Caesium-Oxide Photoelectric Cathodes [and its Variation with Time!—Déjardin and Latarjet, p. 278. Photoelectric Cells using Caesium on Oxidised Silver : Optical Effect of the Silver Oxide.—Ives and Fry, p. 335. Caesium-Oxygen-Silver Photoelectric Cell of High Sensitivity, for Sound Picture Systems.—Kelley, p. 573. Photoelectric Effect of Caesium Vapour.—Kunz, p. 573. New Research on Cathode Rays.—Baird Company, p. 279. A New Multiple Cathode-Ray Oscillograph.—Boekels and Dicks p. 283. Cathodes and the Influence Exerted on Emission by Inclusion

- p. 283. An Investigation of Various Electrode Structures of Cathode-Ray
- Tubes suitable for Television Reception .- Du Mont, p. 220.

- Reception of Television : How the Cathode-Ray Oscillograph can
- be Utilised,—Hardy, p. 512. Static Light/ and Current/Voltage Characteristics as the Basis of Brightness Modulation in Cathode-Ray Tubes [and the Electrical Behaviour of such Tubes compared with that of Gas-Filled

- Behaviour of such Tubes compared with that of Gas-Filled Valves].—Hehlgans, p. 629. Distortions caused by the Space Charge in Cathode-Ray Tubes [and the Use of a Bent Tube].—Hudec, p. 453. Intensity Control of the Gas-Concentrated Cathode Ray by Wehnelt Cylinder.—Kleen, p. 220. Intensity [Brightness] Control of Gas-Concentrated Cathode Rays by Electrical Fields—Wehnelt Cylinder.—Michelssen and Kleen, n. 105.
- by Electrical Pictus Hard **p. 105**. The Construction and Working of a **Cathode-Ray** Oscillograph [with Special Cathode giving Ray of Secondary Electrons by Impact of Positive Ions].—Peters, p. 47. **Cathode-Ray** Tubes costing 75 and 150 Marks.—Pressler Company, 200
- Cathode-Ray Tube containing Two Independent Systems .--- Schles-
- Cathode-Ray Tube containing two independent Systems.—Schlesinger: Loewe Company, p. 168.
 Cathode-Ray Television in which the Ray re-sets itself at End of Line and End of Picture by action on Auxiliary Electrodes on Fluorescent Screen.—Telefunken, p. 168.
 Cathode-Ray Television with Line Change effected by Ray Itself.— Telefortion of the set of
- Telefunken : Ilberg, p. 336. Remarks on W. Heimann's Paper "The Sensitivity of the Braun [Cathode-Ray] Tube with Gas Concentration, at Various Fre-quencies."—von Ardenne : Heimann, p. 172. Cathode-Ray Oscillography [Physical Society Discourse].—Watson
- Watt, p. 224. Cathode-Ray : see also Electron and under "Subsidiary Apparatus and Materials."
- and Materials. Television by Cinematography followed by Scanning and Recording on Gramophone Disc.—Telehor Company, p. 168. Images in Colour : Suggested Method.—Williams, p. 168. Colour Television.—Gouck : Williams, p. 399. Reflecting Values of Colours [Experimental Results].—Wood,

- p. 630. Contact Potential Differences between Different Faces of Copper
- Single Crystals.—Farnsworth and Rose, p. 631. The Photoelectric Effect of Crystals of Argentite, Proustite and Pyrargyrite.—Athanasiu, p. 573.

- The Temperature Dependence of the Crystal Photoelectric Effect.— Barth and Dember, p. 400. Photoelectric Effect in Cuprite Single Crystals.—Deaglio : Dember, pp. 455 and 573. The Crystal Photoelectric Effect in Transparent Zinc Sulphide.— Pember, p. 47. Internal Photoelectric Absorption in Halide Crystals.—Gurney, p. 55
- p. 573.

- p. 573. The Crystal Photoeffect. --Joffé, p. 573. The Photoelectric Effect in Cuprite Crystals.--Joffé, p. 455. The Photoelectric Effect in a Particular Active Layer of the Car-borundum Crystal.--Lossew, p. 455. Crystal Photoelectric Effect in Photoelectrically Conducting NaCl.
- --Pelz, p. 631. On the Movement of Electricity Caused by Light, Heat and Cathode
- Rays in Single Crystals of Galax.—Rup, p. 277. The Theory of the Crystal-Photoeffect.—Teichmann, p. 170. Contilution to the Theory of the Crystal Photoelectric Effect.

- Teichmann, p. 400. The Internal Photoelectric Effect in Crystals.—Wilson, p. 107.
- Crystals; see also Rectification. Behaviour of Electrons and "Holes" [Positive Electrons] in [Illuminated] Cuprous Oxide.—Joffa, Nasledov and Nemenov,

- Illuminated] Cuprous Oxide.—Joffa; Nasledov and Nemenov, p. 632.
 The Nature of the Spontaneous Currents Occurring on Illumination of Valious Detector Substances.—Waibel, p. 47.
 Remark on the Paper by F. Waibel, On the Nature of the Spon-taneous Current given by Illumination of Various Detector Materials.—Rupp, p. 170.
 The Phonovisograph [for Simultaneous Disc Recording of Sound and Television].—Wollmann, p. 168.
 Elimination of Echo Effects in Phototelegraphy by Automatic Threshold Regulation on Receiver.—Telefunken: Schröter and Federmann, p. 336.
 The Influence of Matter on Very Slow Electrons, investigated Photo-electrically.—Lang, p. 456.
 Electrons and Electron Optics : see also under "Subsidiary Appa-tatus".

- ratus.
- ratus. Photoelectric and Metastable Atom Emission of Electrons from Surfaces in the Rare Gases.—Kenty, p. 278. The Occurrence and Explanation of the Selective Emission of Photoelectrons at Composite Alkali Cathodes.—Kluge p. 221. Photoelectric and Thermionic Emission from Composite Surfaces.—
- Notingham, p. 47. Energy Distribution of Photoelectrons from Zinc Surfaces.— Bradbury, p. 455. Theory of the Energy Distribution of Photoelectrons.—Du Bridge,
- pp. 170 and 455.

Phototelegraphy and Television.

- Television at the Berlin Radio Exhibition, 1932: Television from the Witzleben Ultra-Short-Wave Transmitter.—Kette: Kirschstein, p. 46.
- The Special German P.O. Section for Television at the 9th Great German Radio Exhibition.—Kette, p. 46. Television at the 1932 Berlin Radio Exhibition.—Traub, pp. 108
- and 630.
- and 630. Television Exhibition, pp. 336 and 399 (two). The Dependence of the Optical Threshold of the Eye on the Visual Angle, and Its Relation to the Visibility of Weakly Lit Elements in Television Reception.—Peters, p. 630. The Eye : a Link in the Television Chain.—Wright, p. 108. Switching Arrangement at Facsimile Receiver to ensure a Strong Start-Stop Signal without Too Strong a Picture Signal.—Siemens & Helvie a. 167
- & Halske, p. 167. Fading Elimination, especially in Phototelegraphy.—Int. Gen.
- Elec., p. 279.
- Elec., p. 279.
 The Photoelectric Properties of Alkali Metal Films as a Function of Their Thickness.—Brady, p. 107.
 The Action of a Beam of Periodic Light on Some Metallic Films.— Majorana, p. 278.
 Optical and Photoelectrical Investigations of Thin Metallic Films.— Conduct a 170.
- Schulze, p. 170. The [Constant Quantic] Efficiency of Fluorescence of Sodium Salicylate.—Dubouloz, p. 454. The Determination of the Highest Frequencies to be Transmitted and the Influence of Phase Distortion in Television.—Fayard,
- and the function of Phase Disorbition in Provision. Paylar, p. 399.
 Light Emission from Gas Discharges especially from Resonance Lines [Theoretical and Experimental Treatment of Neon Sodium Vapour Lamp, etc.]. de Groot, p. 168.
 The New Gas Discharge Tubes, and Their Application to Television.
- -Harris, p. 278. The Importance of the High Frequency Gas Discharge for Tele-

- The Occurrence of Image Errors in relevision, Phototelegraphy, etc. --Thun, p. 631. The New Continuously-Working Intermediate-Film Television Transmitter of the Fernseh A.G.—Schubert, p. 630. The Baird Grid [Kerr] Cell, p. 278. The Te-Ka-De Crystal Light Relay [replacing Kerr Cell].—von Okolicsanyi, p. 630. New Optical Assembly for Television Projection Receivers [Kerr Cell Equipment using both Ordinary and Extraordinary Rays].— Levin p. 573.

- New Optical Assembly for Factorian Frogenium Recordinary Rays].— Levin, p. 573.
 Light Modulation. Improved Method for Use in Television— Brighter Images [Use of Kerr Cell without Nicol Prisms].— Myers: Wilson Laboratories, p. 106.
 A Note on the Kerr Cell [and the Distortion due to the Curvature of Its Characteristic].—Wright, p. 512.
 A Method of Measuring the Maximum Intensity of Light from the Photoflash Lamps or from Other Sources of Short Duration.— Forsythe and Easley, p. 43.
 A New Crater Point Lamp.—Mervyn Company, p. 106.
 White Light for Television [a New Mercury Lamp excited by Electrodeless Discharge].—Peck: Myers, p. 168.
 Considerations on the Latest Methods of Generating Light [including the Sodium Vapour Lamp for Television, etc.].—Pirani, p. 512.
 Television Reception with Mirror Helix and Mercury-Argon Lamp fed with High Frequency Current.—Scholz, p. 48.
 Sodium-Vapour Lamps.—Wertli: Philips Company, p. 106.
 New Lamp for Sourd-Recording and Television [Mercury Vapour, with Grid], P. 168.

- with Grid], p. 188. Lamps: see also Gas Discharge, Light Sources, Modulated, Projection.

- jection.
 Plano-Convex Water Lens in front of Television Screen to give "Depth" to the Image.—Myers, p. 168.
 Measurements on the Effect of Light on Spurious Contact Potentials and "Trapped" Electrons.—Nottingham, p. 631.
 Crystal Light Relay: see under Kerr Cell.
 New High Intensity Light Sources for Television Receivers [especially the "Linear" Lamp for Mirror Helix, with Modulated D.C. to Internal Electrodes and R.F. Control to External Ring Electrodes].—Scholz: Leithäuser, p. 48.
 New American Light Sources for Television Receivers : the Weiller Hot-Cathode Crater Lamp, and a Mercury-Arc Tube with Very Short Arc whose Light is conducted to Scanning System through Quartz Rod, p. 630.
- Short Are whose Light is conducted to Scanning System through Quartz Rod, p. 630. The Practical Realisation of Thun's "Line Control" [Variable Spot Speed Principle] with the Application of Newly Developed Methods.—von Ardenne, p. 46. The Thun "Line Control" System [Variable Speed Scanning], p. 454. The Low Frequencies in the Television Image Currents.—Kirsch-ctein, 621.
- stein, p. 631. The Photoelectric Sensitivity of Magnesium.—Cashman and Huxford
- p. 455. Photoelectric Properties of Magnesium .- Déjardin and Schwegler
- pp. 455 and 631.

- The Photoelectric Effect at Magnesium Surfaces .-- Gerding and Gerding-Kroon, p. 278. Demonstration of Marconi Television [at British Association Meet-

- Demonstration of Marcon Television (at Drillsh Association Intering), pp. 46 and 108 (two).
 Marconi Television Transmitter Type TT5.—Kemp, p. 220.
 A More Compact Mirror Drum ?—Everett, p. 279.
 Mirror Drum Scanning : the Optical Efficiency.—Wilson, p. 399.
 The Balancing of Mirror Drum and Nipkow Disc on Same Axle.—
- Lecuyer, p. 630. Brightness Relations in Mirror-Wheel Reception : Correspondence.
- -Papst : Kirschstein, p. 630. The Production of Modulated Light.-Wataghin and Deaglio,
- The Production of Modulated Light, watashin and Despite,
 p. 106.
 The Suitability of "Series Modulation" ["Constant Potential" Modulation] for Television Transmission.—Ditcham, p. 399.
 Modulation Frequencies in Visual Transmission.—White, p. 220.
 The Thermionic and Photoecetric Work Functions of Molybdenum.
- -Du Bridge and Roehr, p. 47. Some Distant Receptions of Television Transmissions from London [and the Occurrence of Multiple Images] .--- Bodroux and Rivault,
- [aid the Content of Multiple Images]. Doublet and Revalle,
 p. 572.
 On the "Hunting " of Nipkow Discs.—Haefer and Möller, p. 106.
 Noise as a Limiting Factor in Amplifier Design [with Special Reference to Television].—Keall, p. 631.
 Sight and Sound on One Wave.—Peck : Columbia Broadcasting Company, pr. 46, and 199
- Company, pp. 46 and 108. Sight and Sound on One Wave [Sound Impulses converted into Light Impulses which are used as part of the Scene to be Televised].— Wood, pp. 279 and 399.
- Sustained Oscillations [from a Photoelectric Cell Circuit] .- Hochard,
- p. 391. Photoelectric Conduction and Absorption in Lenard Phosphorescent Materials in the Red and Infra-Red Regions of the Spectrum .-
- Weber, p. 456. Investigation of Barrier-Layer Photocells [Effects of Electrode Thickness and of Nature of Gas used in Sputtering Process, etc.]. —Borissow, Sinelnikow and Waither, p. 400. Electrical Characteristics of Barrier-Layer Photocells.—Gleason,

- p. 631.
 The Dependence of the E.M.F. of Copper Oxide [Barrier Layer]
 Photocells on the Intensity of Illumination and Wavelength.—
 Goldmann and Lukasiewitsch, p. 220.
 The Frequency Variation of the Barrier-Layer Photocell.—Görlich,

- The Frequency Variation of the Barrier-Layer Photocell.—Gorlich, p. 336.
 Reversal of Current in Rectifier Photocells.—Guild, p. 277.
 Radio Tubes used as Photocells.—Koechel, p. 169.
 Non-Additive Effect of Different Radiations on Copper Oxide Photocells.—Lapique, p. 454.
 Reversal of the Current from a Cuprous Oxide Photocell in Red Light.—Poole and Atkins, p. 221.
 Reversal of Current in Rectifier Photocells.—Poole and Atkins, p. 454.
- p. 454.
- p. 454.
 Experiments on the Suitability of Some Rectifier Photocells for the Measurement of Daylight.—Poole and Atkins, p. 454.
 Self-Generating Photocell [Dry-Disc Cell giving 5-7 Milliamperes in Direct Sunlight].—Rhamstine, p. 221.
 On the Proof of a Boundary Layer in Cuprous Oxide Barrier-Layer Photocells.—Rother and Bomke, p. 400.
 Photocells.—Rother and Bomke, p. 406.
 The Equivalent Circuit of a Blocking-Layer Photocell.—Wood, pp. 336 and 631.
 Good Matching Conditions for Low-Resistance Barrier-Layer Photocell by use of Magnetron in First Amplifier Stage.—Zeiss Ikon, p. 573.

- Photocell by use of Magnetron in First Amplifier Stage.—Zeiss Ikon, p. 573.
 Photocells and Their Applications.—Zworykin and Wilson, p. 454.
 Photocells and Amplifier Combination with Very Short or No Connecting Leads, by use of Valve with External Control Electrode.—Tonbild-Syndikat, p. 454.
 Photo-Conductivity [Survey, with Bibliography of 189 Items up to 1982].—Nix, p. 47.
 On the Confirmation of the Existence of a New Photoelectric Phenomeneous Different of Intermittent Illumination on This Pletinum
- The commence of a result of a

- and Smith, p. 169. The Bernheim Photoelectric Cell Functioning without Current Amplificatiom.—Bernheim : G. Mazo Company, p. 512. Oxide-Film [Barrier-Layer] Photoelectric Cells.—Bloch, p. 400. Contribution to the Study of Gas-Filled Photoelectric Cells.— Boutry, p. 169.
- Recent Improvements in Photoelectric Cells.—Campbell, p. 169. Modern Methods of Manufacturing Photoelectric Cells.—Déjardin,
- pp. 169 and 221.
- pp, 169 and 221. The Use of Colour Filters, controlling Part only of Sensitive Surface, to make Spectral Sensitivity of Photoelectric Cell similar to that of the Eye.—Dresler, p. 454. On a Working Régime of Gas-Filled Photoelectric Cells [the Hemi-spherical Dunoyer Cell "SCAD Series S"].—Dunoyer and Decured r 2009 Paounoff, p. 278 .

Phototelegraphy and Television.

- The Effect of a Magnetic Field on a Gas-Filled Photoelectric Cell .----Fourmarier, p. 168.
- Fourmarier, p. 108.
 The Copper-Cuprous-Oxide Rectifier and Photoelectric Cell.— Grondahl, p. 515.
 A New Use for Old Valves [as Photoelectric Cells, through Action of Magnesium Deposit].—McCarthy, p. 169.
 Inertia Effects in Gas-Filled Photoelectric Cells.—Ollendorff, p. 107.
- Inertia Erects in Gas-Fulled Photoelectric Cells,—Ollendorff, p. 107, Photoelectric Cell replaced by Discharge Tube containing Atoms in Metastable State [Neon with Argon Admixture, using Neon Light Scanning].—Philips Company, p. 169, Photoelectric Cells for Ultra-Violet Light.—Rentschler, Henry and Smith, p. 400.

- Smith, p. 400.
 Photoelectric Cells: Their Properties and Uses.—Stoodley, p. 335.
 Spectral Sensitivity Curves of Sodium, Cadmium, and Titanium Photoelectric Cells.—Taylor, p. 278.
 Photoelectric Cell with Grid for Carrier Frequency, used in Com-pensation Circuit so that no A.C. flows in External Circuit in absence of Illumination.—Telefunken: Schriever, p. 278.
- An Extraordinary Photoelectric Cell, p. 277. "Visitron" Photoelectric Cells with Normal Sensitivities from 100 to 150 Microamperes per Lumen, p. 277. Photoelectric Cells: see also Caesium, Photoelectric Tubes, Photo-cell, Photoemissive, Photovoltaic, Photoronic, Selenium, Theoremissive, Photovoltaic, Photoronic, Selenium,
- Television
- Photoelectric Currents in Gases between Parallel Plate Electrodes.-Young and Bradbury, p. 221.
- The Selective Photoelectric Effect [Comprehensive Survey].— Déjardin, p. 107. The External Photoelectric Effect in Alkali Halides.—Fleischmann,
- p. 631. Theory of the Complex Photoelectric Effects.—Goldstein, p. 573
- Theory of the Complex Photoelectric Effects.—Goldstein, p. 573. Influence of the Metal Surface on the Position of Selectivity in the External Photoelectric Effect, and The Selective Behaviour of Alloys in the External Photoelectric Effect.—Hlučka, p. 631. Connection between Natural Vibration and Selective External Photoelectric Effect.—Hlučka, p. 335 (two). The Periodic Photoelectric Effect of Thin Layers with Mono-chromatic Illumination.—Hlučka, p. 335. A New Type of Photoelectric Effect in Cuprous Oxide in a Magnetic Field—Kikoni and Noskow p. 454

- A New Type of Photoelectric Effect in Cuprous Oxide in a Magnetic Field.—Kikoin and Noskow, p. 454. The Internal Photoelectric Effect in Semi-Conductors, and the Hall
- Effect.—Kikoin and Noskow, p. 336. Experiments on the Selective Photoelectric Effect and the Optical Absorption at Compound Photoelectric Cathodes.—Kluge, p. 107.
- The Optical Absorption at Surface Films with Doubly Selective Photoelectric Effect.—Kluge, p. 573. Conservation of Energy and Impulse in the Photoelectric Effect.—
- Kunz, p. 456.
- The Internal Photoelectric Effect in Liquid Dielectrics .- Liandrat, p. 455. Recent Developments in the Study of the External Photoelectric
- Effect,-Linford, p. 400. The Photoelectric Effect of Electric Spark Radiation.-Meiklejohn,
- p. 222.
 The Internal Photoelectric Effect of Gamma Rays.—Meitner and Kan Chang Wang, p. 632.
 Existence of an Internal Photoelectric Effect in Cuprous Oxide.—
- Nasledow and Nemenow, p. 277. The Photoelectric Effect in the [Copper Oxide/Zinc] Barrier Layer on Irradiation by Ultra-Violet Light.—Nasledow and Nemenow,
- p. 336.
 The Question of the Internal Photoelectric Effect in Cuprous Oxide. —Nasledow and Nemenow, p. 400.
 Investigations of the Internal Photoelectric Effect in Metals.—
- Schulze, p. 455. Calculation of the Long-Wave Limit of the Photoelectric Effect from the Atomic Volume of the Elements.—Schweikert, p. 107. The Photoelectric Effect in a Silicon Carbide Detector.—Specht,
- p. 631. Angular Variation of the Photoelectric Effect on Insulators in
- Polarised Light.—Spies, p. 573. On the Occurrence of the Spectral Selective Photoelectric Effect at Thin Alkali Metal Films.—Suhrmann and Schallamach, p. 107.
- he Question of the Existence of a Barrier-Layer Photoelectric Effect in Lead Sulphide.—Tiede and Brückmann, p. 221.

- Effect in Lead Suiphide.—1 iede and Brückmann, p. 221. The Influence of Oxygen and Sulphur on the Photoelectric Effect in Alkali Metals—k and Na.—Timofeew and Nalimow, p. 400. Photoelectric Effect : see also Crystal, Detector, X-Ray. Photoelectric Emission in a Magnetic Field.—Schmid, p. 335. Extension of Fowler's Theory of Photoelectric Sensitivity as a Function of Temperature.—Waterman and Henshaw, p. 574.
- Note on Rating of Photoelectric Tubes [and the Effect of the Tem-perature of the Light Source].—Koller, p. 169. On the Conditions Necessary for the Occurrence of an Independent
- Photoelectric Voltage.—Teichmann, p. 48. The Chemical and Physical Conditions of the Photoelectrically Active Hydrogen Load of Platinum and Palladium.—Bethe, p. 278.
- Effect of Temperature on the Energy Distribution of Photoelectrons. -Roehr and Du Bridge, p. 631.
- The Passage of Photoelectrons through Mica.-Bradbury and Young, p. 222.

- Comparison of Photo-Emissive, Photo-Conductive and Photo-Voltaic Cells.-McMaster, p. 573.
- Phototelegraphy of Half-Tone Pictures by Multiple Modulation of a Short Wave ---- Telefunken : Schröter, p. 453. Short Wave.—Telefunken : Schröter, p. 453. The Rôle of Colouring Matter in Photovoltaic Phenomena.—Stora,
- p. 455. Sensitivity, along the Spectrum, of Photovoltaic Cells with Copper
- Electrodes covered with Sub-Oxide of Copper.-Athanasiu, p. 169.
- On the Differentiation between the Electronic and the Photoelectro-chemical Effects in Photovoltaic Cells, --Audubert, p. 278. Photovoltaic Cells and Their Applications. --Boutaric : Audubert,
- p. 336. Papers on Photovoltaic Cells of Salts of Copper.-Audubert, p. 455.
- Comparative Characteristics of the Copper Oxide and "Photonic" Cells: The Weston Photronic Cell in Optical Measurements: A
- New Photo-Cell Photometer [using two Photoronic Cells],— Bartlett: Shook and Scrivener: Gleason, p. 47. The Variation in Sensitivity of the Photronic Cell with X-Ray Wavelengths.—Gleason, p. 631. Notes on the Weston Photonic Photoelectric Cell.—Romain:

- Bartlett, p. 277. Aspects of the Transmission and Reception of Still Pictures.--Tweed, p. 47.
- Polarising Louvres and Their Application [to replace Nicol's Prisms].

- Bolarising Lowres and Their Application [to replace Nicol's Prisms].
 —Smith, p. 573.
 Design for Projection Apparatus [using the Crater Type Neon Lamp].
 —Mervyn Company, p. 168.
 Photoelectric Quantum Counters for Visible and Ultra-Violet Light: Part I.—Locher, p. 170.
 [Television] Progress at Radiolympia, p. 630.
 Photoelegraphic Recorder with Stylus tracing a Sine Wave of Amplitude dependent on the Absorption offered to the Scanning Light Spot.—Brulin, p. 632.
 A.C Rectification by Photosensitive Aggregates [Objections to Eccles's Thermoelectric Theory of Ciystal Detector: New Theory].
 —Reflecting Values of Light.—Wood, p. 279.
 Contribution to the Determination of the Reflection Coefficients of Metals for Visible and Ultra-Violet Light.—von Fragstein, p. 455.
 An Electro-Optical Relay using a Quartz Resonato with Uniform Response over a Wide Range of Frequencies.—Guerbilsky, p. 512.
 The Determination of the Limiting Photoelectric Wavelength for Rhenium.—Engelmann, p. 573.
 Sixty-Line Seanning : Demonstration at University College, p. 399.
 A. Nuw, Wethold, F. Berge Generic, Transmissing Values of Light.

- Rhenium.—Engelmann, p. 573.
 Sixty-Line Scanning : Demonstration at University College, p. 399.
 A New Method of Beam-Scanning Transmission [based on the Ulbricht Sphere Principle used in Photometry].—Möller, p. 630.
 Is the Scanning Disc Obsolete ?—Barton Chapple, p. 107.
 Scanning Disc with Two-Turn Spiral, combined with Half-Speed Disc with Spiral Window: Small Diameters without Loss of Brightness.—Barthélemy. p. 454.
 Scanning System allowing the use of Ordinary Talking Films for both Picture and Voice Transmission.—Peck, p. 399.
 Experiments and Measurements with Selenium Barrier-Layer Photocells.—Bergmann, p. 335.
 Chrom-Selenium Photocells.—Fink and Alpern, p. 169.
 The Dependence of the E. M.F. of Selenium Barrier-Layer Photocells on the Intensity of Illumination.—Goldmann, p. 221.
 The Selenium Photo-Element and Its Applications.—Schwandt, p. 47.

- p. 47.
- Selenium Cell employing New Principle.—Süddeutsche App., p. 221. The Becquerel Effect at Selenium Electrodes.—Volmer and Moll,
- p. 278.
- p. 278. The Conductivity of Electronic Semi-Conductors in a Magnetic Field.—Bronstein, p. 400. The Discontinuities of Potential at the Contact of a Semi-Conductor and a Metallic Electrode.—Déchéne, p. 455. Electrical and Optical Behaviour of Semi-Conductors. IX. Mec-hanism and Origin of Conductivity in the Dark and Photo-electric Conductivity of Cuprous Oxide.—Engelhard, p. 631. Report on the Theory of Semi-Conductors.—Fowler, p. 515. Electrical and Optical Behaviour of Semi-Conductors. VII.— Photoelectric Properties of Semi-Conducting Barrier Layers.— Leo. p. 107.

- Leo, p. 107. Electrical and Optical Behaviour of Semi-Conductors. VIII.—A Method for the Measurement of Photoelectric Currents in Semi-Conductors.—Schönwald, p. 107.
- Shot Effect and Thermal Noise in the Photocell Amplifier.—von Orbán, p. 334. Photoelectric Measurement of the Shapes of Solar Absorption
- Lines.—Dunham, p. 632. Standing Light Waves : Repetition of an Experiment by Wiener, using a Photoelectric Probe Surface.—Ives and Fry, p. 335. Retinal Rivalry as a Neglected Factor in Stereoscopic Vision.—
- Washburn, p. 630.
- Hand Synchronisation.—Carmichael, p. 168.
 Synchronisation of D.C. Motor by Tuning Fork driven by Magnet Poles on Shaft of Motor itself.—Thomson-Houston Company, p. 336. Synchronisation in Television [including Description of the Marconi
- Method] .--- Walker, p. 399.

Phototelegraphy and Television.

- A Synchronising System for Electrical Transmission of Pictures .--Niwa, p. 108.
- The present Position of Telefunken Television Broadcasting .-
- The present Postula of Leterative Version 2015 Schröter, p. 629. "Self Centred." Television.—De Wet, pp. 108 and 279. A New [Television] System ? [Numerous Photo-sensitive Elements each controlling Amplitude of One Particular Note: Corre-sponding Conversion at Receiver].—Owen, p. 108. Survey of the Development and Present Position of Television.—
- Kette, p. 630.
- Developments in Television [including Telefunken Results with Mirror Helix and Intermediate Film, using 7 Metre Wave].—
- Lance, p. 108. Television [Survey for 1932].—Mitchell, p. 220. A Contribution to the Development of Practicable Television Systems.—Thun, p. 630. The Problems of Television [including mention of a New Photo-elevision for Levision fincluding mention of a New Photo-
- electric Cell, Cable for Frequencies up to 500 kc/s, etc.].-Walton, p. 107.
- Big Events in 1932 : a Year of Progress [in Television]. p. 108
- Television Developments : Great Britain-Germany-United States, p. 46.
- Television in America To-day [including Details of the Farnzworth Cathode-Ray "Dissector" and "Oscillite" Tubes].-Dinsdale, 108.
- p. 198. Television in Holland.—Witsenberg, p. 108. Theoretical Notes on Certain Features of Television Receiving Circuits [including Correction of Resistance-Coupled Amplifiers by Addition of Small Amounts of Inductance].—Robinson, p. 512. Two Way Television as a Public Utilit Court
- Two-Way Television as a Public Utility Service.—Wilson, p. 279. The Use of the Cathode-Ray Oscillograph at Ultra-High Frequencies.

- -Hollmann, p. 634. A Study of the Propagation of [Ultra-Short] Wavelengths between
- Three and Eight Metres.—Jones, p. 334. The First **Ultra-Short** Wave Television Receiver on the Market.-
- Noack, p. 453. Notes on Propagation of Waves below Ten Metres in Length [Ultra-Short Waves].—Trevor and Carter, p. 334. Television Tests on Ultra-Short Waves from Empire State Building,

- Television Tests on Ultra-Short Waves from Empire State Building, p. 220.
 A Photoelectric "Valve."—Kunz and Tykociner, p. 631.
 Ships at Sea get Weather Maps of Whole Ocean.—RCA, p. 167.
 Photoelectric Investigation of the Temperature Variation of the Electronic Work Function at a Nickel Surface Covered with Atomic Barium.—Suhrmann and Deponte, p. 632.
 Variation of Photoelectric Efficiency with Work Function in the Extreme Ultra-Violet.—Kenty, p. 455.
 On the Work-Functions of Electrons Emitted from Metals.—Tamm and Blochinzev, p. 47.
 The Response of Barrier-Layer Photo-Cells to X-Rays.—Gleason, p. 455.

- The Response of Barner-Layer Photo-Cens to A-Rays.—Gleason, p. 455. The Saturation Current in the Photoelectric Conductivity of X-Rayed Rock Salt.—Kalabuchow, p. 277. On the Classical Distribution of Electrons in the Photoelectric Effect of X-Rays.—Kunz, p. 455. The Electron Emission from Metals under the Action of X-Rays.—
- Kiistner, p. 48. On the Behaviour of Barrier-Layer Photoelectric Cells on Exposure to X-Radiation.—Scharf and Weinbaum, pp. 277 and 454.

MEASUREMENTS AND STANDARDS

- A New A.C. Measuring Set based on the Principle of the Potentio-meter [using a Vacuum Thermo-junction carrying a Current kept constant by a Potentiometer Device].—Tanaka and Sakai, p. 51.
- Arrangement for Measuring the Amplifying Power of H.F. Amplifiers.—Telefunken and Runge, p. 574. Amplifiers : see also Transmission Equivalent.

- Ampiners : see also Fraismission Equivalent. Pointer Instruments for Beat-Note Methods of Measurement [including Harmonic Analysis].—Laible, p. 110. Beat-Note Methods of Measurement and Their Liability to Error [including the "Double-Beat" Method].—Subra, p. 633. Bridge Methods for Measurements at Radio Frequencies.—Burke,
- p. 51.

- p. 51.
 A Radio-frequency Bridge for Impedance and Power-Factor Measurements. —Dye and Jones, p. 337.
 Alternating-Current Bridges for Measurements of Electrical Insulating Materials.—Ford and Reynolds, p. 223.
 The Thompson Bridge for Direct Current.—Krönert, p. 51.
 The Convergence of Successive Measurements in Bridge Methods.— Kupfmiller, p. 634.
 On the A.C. Bridge with Instrument Transformers, and Characteristics of Each of its Elements.—Kuriyama, p. 513.
 Accidental Errors in A.C. Bridges [Reduction of Errors by a "Method of Repetition."].—Ogawa, p. 513.
 Bridge for Measuring a Billion Ohms with 1 Volt impressed : using the General Electric FP-54 Four Electrode Valve.—Saxl, p. 634. p. 634. The Brownian Motion of the Resonance Radiometer,---Van Lear,
- p. 223.

- Note on an Improved Form of an Induction Coil Buzzer [as A.C. Source for Resistance Measurements using Special A.C. Galvano-meter as Null Iniciator].—Mukherjee, p. 576. The Standards of Capacitance at the Physikalisch-Technische Reichsanstalt.—Giebe and Zickner, p. 338. Exact and Absolute Measurement of Small Capacities.—Clay,
- p. 49.
- Direct-Reading Phonic Capacity Meter [Oscillating Neon Tube Method].—Durepaire, p. 633. Measurement of Small Capacities.—Lampe, p. 110. A New Method of Measuring Capacities at High Frequencies.—
- Schmidt, p. 337.
- Triode Instruments for the Measurement of Capacity, with Pro-portional Scales and Direct Reading.—Vecchiacchi, p. 49. The Industrial Measurement of Capacity and High Resistance.—
- The Industrial Measurement of Uapacity and High Kesistance.— Regoliosi, p. 633. Determination of the Chemical Composition of Liquids by Electrical Resistance Measurements [Using the Geyger "Iron Ring Quotient Meter"].—Geyger, p. 457. The Calculation of Air-Cored Protecting Chokes.—Edler, p. 633. Empirical Formulae for the Calculation of Air-Cored Chokes.—
- Hak, p. 633.
- Tak, p. 603. The Calculation of Iron-Free Choking Coils [Simplified Method allowing for Heating Effects].—Edler, p. 576. Chokes: see also Coils, and under "Subsidiary Apparatus" (Chokes, Coils, Iron-Cored).
- Synchronisation of Clocks over Telephone Network .- Brillié Frères,
- p. 223. The Clinker Electric Clock for Mains which are not Time-Controlled. -British Thomson-Houston Company, p. 223. Radio Clock System Patented --McCann, p. 338, A Speaking Clock [for Use on Telephone Network].
- Nimier, p. 50. Quartz Clocks as Time Standards [Critical Discussion] .- Scheibe, p. 633.
- p. 633. A Quartz Clock for Very Exact Measurements of Time and Fre-quency.—Scheibe and Adelsberger, p. 109 (two). Crystal-Controlled Clock with Quartz vibrating at such a Low Rate as to require No Frequency Reduction.—Sollenberger, p. 457.

- p. 457. A New Type of Free-Pendulum Clock.—Tomlinson, p. 223. A New Electric Pendulum Clock.—W. Zeh Company, p. 109. Clocks: see also Frequency, Time. The Calculation of Air-Cored Single-Layer Coils [Formula for Least Length of Wire].—Edler, p. 49. The Fflect of Displacement Currents on the High-Frequency Resistance of Circular Single-Layer Coils.—Palermo, p. 172. A New Abac for Single-Layer Coils.—Seki, p. 172. A Quasi-Stationary Calculation of the Natural Wavelengths of Single-Layer Flat and Cylindrical Coils.—Zuhrt, p. 633. Coils: see also Chokes.
- Single-Layer Flat and Cylindrical Coils.—Zuhrt, p. 633.
 Coils: see also Chokes.
 The Measurement at High Frequencies [above 1 Mc/s] of the Loss Angles of Condensers).—Rohde and Schlegelmilch, p. 512.
 The Complete Field Distribution in a Cylindrical Conductor of Circular Cross Section composed of an Inner Conductor of One Material and an Outer Sheath of Another, for an Alternating Current in an Axial Direction.—Fischer, p. 171.
 A Wide-Range Coupling Meter for Inductive, Capacitive and Real Couplings.—Wirk: Siemens & Halske, p. 633.
 AEF Provisional Resolutions on the Names and Definitions of Various Types of Electric Current and Voltage and Phase at High Frequencies.—Ruelle, p. 514.
 A Method of Damping Measurement for Oscillatory Circuits [using a Quartz-Controlled Signal Generator].—Petržilka and Fehr, p. 48.
 Dynamic Measurement of Electron Tube Coefficients.—Tuttle,

- Dynamic Measurement of Electron Tube Coefficients .-- Tuttle,
- p. 506.
- Crystal Control applied to the Dynatron Oscillator .- MacKinnon, p. 155.
- p. 155.
 The Definition and Measurement of the Resistance of an Earth Connection.—Bigorgne and Marzin, p. 513.
 The Measurement of the Resistance of Earths by the Mocquard Apparatus.—Bridoux: Mocquard, p. 518.
 The Resistance of Earth Electrodes.—Morgan and Taylor, p. 505.
 A Geophysical Earth Tester [Modification of "Megger"] p. 513.
 Earth-Resistance Meter with Greatly Increased Sensitivity.— Prior 624

- Pflier, p. 634.
- Some Recent Earth-Resistivity Measurements in the United States. -Card, p. 634.
- dard, p. 634.
 A New Exposition of Electromagnetic Phenomena : the Uselessness of the Idea of Magnetic Mass. Vasilesco-Carpen, p. 456.
 On the Use of the Vacuum Tube Electrometer with Extremely High Input Resistance. Burroughs and Ferguson, p. 634.
 The Use of Vacuum Tube Electrometers for Measuring the Potentials
 Use of Vacuum College Descent and Event and Even and E
- of High-Resistance Cells.—Burroughs and Ferguson, p. 172. A Sensitivity Control for the Lindemann Electrometer.—Grimmett,
- p. 223. The Double-Thread Electrometer as an A.C. Voltmeter at High Fond Ultra-High] Frequencies.—Nissen, p. 574. Webpelt and
- Ind Ultra-High Frequencies.—Nissen, p. 574. Braun Electrometer with Fibre Suspension.—Wehnelt and А
- Johannesson, p. 634.

Measurements and Standards

- A Practical Vacuum-Tube Circuit for the Measurement of Electromotive Force [without "Electrometer" Valves].—Ellis and Kiehl, p. 337.
 Erroneous Loss-Angle Measurements due to Capacity Changes [from Small Corona Effects, etc.] during the Period of Application of A. C. Voltage.—Tschiasany, p. 634.
- Correction of Frequency Error in Moving-Iron Voltmeters.—Camp-bell: Carter: Gall, p. 634. Errors in Voltage Measurements due to Earth Capacitances.—Starr,
- p. 634. Field Instruments [and Methods of Meeting their Special Require-
- ments].—Gall, p. 634. A Field-Intensity Meter [using a Modified Superheterodyne Circuit].
- -Brown and Koehler, p. 48. A Field-Intensity Set [for both Ground and Sky Waves, and Some Results].-Green and Wood, p. 574.
- Recording Field Strength: Equipment used by the B.B.C. for Automatic Measurement.—Smith, p. 170. A Note on an Automatic Field Strength and Static Recorder .-
- Mutch, p. 222 Field-Strength Measuring Set for Motor-Car Transport, and Results
- obtained —David —David p. 457. Portable Long Wave Testing Apparatus [Field-Strength Measuring Set].—de Coutouly, p. 233. Some Methods of Stabilising the Frequency of Radio Oscillators.—

- Some Methods of Stabilising the Frequency of Radio Oscillators.— Bruzau, p. 109. Change in Schedule of Radio Transmissions of Standard Frequency. —Bureau of Standards, p. 401. The Stabilisation of Frequencies and Their Exact Measurement [Survey].—Decaux, pp. 338 and 401. Frequency Measurements at Radio Frequencies : Bulletin 10.— General Radio, p. 401. Precise Frequency Measurement.—Giebe, p. 401. The Simplification of Accurate Measurement of Radio-Frequency. —Griffiths p. 456

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 The Absolute Measurement and International Comparison of Frequencies.—Groszkowski, p. 110.
 A Differential Frequency Indicator [for Monitoring Purposes].— Groszkowski, p. 401.
 The Simplification of Accurate Measurement of Radio-Frequency [Comparative Merits of Crystal-Controlled and Fork-Controlled Multivibrators].—Hartshorn : Griffiths, p. 514.
 A New Method of Absolute Measurement of Frequency [Photo-graphing Phase Shift at Each Second Signal of Chronometer].— Kono. n. 49.

- graphing Phase Shift at Each Second Signal of Chronometer, Kono, p. 49. The Micrometer Frequency Meter.—Lampkin, p. 576. A Standard of Radio Frequency [Quartz-Driven Clock : the Neces-sity of devising a Ball Thrust Bearing to replace the Jewel Bearing].—Steel, p. 457. Combining the Frequency Meter and Monitor : Adding an Output Detector to the Electron-Coupled Frequency Meter.—Houldson : Schnell p. 171
- Schnell, p. 171.
- Schnell, p. 171.
 A Frequency Monitoring Unit for Broadcast Stations [Western Electric No. 1-A Unit].—Coram, p. 174.
 R.F. Frequency Response Curves of Tuned Circuit, Tuned Transformer, Amplifier or Complete Receiver, Rapidly Obtained by Visual Method.—Schuck, p. 49.
 A Precision Tuning Fork Frequency Standard [including the use of Maginvar].—Nortman, p. 170.
 Damping and Resonance with an Einthoven String Galvanometer.—Bebb, p. 280.

- I.E.E. Meter and Instrument Section : Charman's Address.— Spilsbury, p. 223.
 A New Impedance Measuring Device [Zero Beat observed by intro-ducing a Third Signal].—Barber, p. 633.
 Measurements of the Characteristic Impedance and Apparent Impedance of Symmetrical and Unsymmetrical Overhead Lines at High Frequencies [in Connection with the Propagation of Interference with Recorderst Resention].—Clausing p. 929.
- at righ rrequencies in connection with the Propagation of Interference with Broadcast Reception.—Clausing, p. 222. Measurements of Impedances.—Starr, p. 110. A Note on Impedance Measurement [American Three-Winding Transformer or Hybrid Coil Method].—Starr, p. 110. Simplifying the Practical Use of the Starr Impedance Measuring Cott Statement and
- Set .- Steffensen, p. 49. Impedance Measurements.—Walsh: Starr, p. 337. The Self and Mutual Inductances of Long Concentric Multi-Layer
- Solenoids .--- Janet, p. 456.

- The Fundamental and Harmonic Frequencies of Multi-Layer Inductance Coils.-Korn, p. 576. Engineering Calculation of Inductance and Reactance [at Low
- Frequencies] for Rectangular Bar Conductors.—Schurg, p. 576, A Simplified Precision Formula for the Inductance of a Helix with Corrections for the Lead-In Wires.—Snow, p. 49, The Bearing of the Earth's Internal Magnetic Permeability upon the Self and Mutual-Inductance of Coils Wound on its Surface.—

- Ine Bearing of the Earth's Internal Magnetic Permeability upon the Self- and Mutual-Inductance of Coils Wound on its Surface.— Swann, pp. 49 and 110.
 On the Use of Arithmetico-Geometric Mean Series for the Calcu-lation of Elliptic Integrals, with Special Reference to the Calculation of Induction.—Grover, p. 456.
 On some New Formulae for the Calculation of Self and Mutual Induction of Coaxial Circular Coils in Terms of Arithmetico-Geometrical Scales.—King. p. 456.
 Inductance and Induction : see also Choking, Coils, Mutual. An Instrument for the Measurement of Dielectric Loss in Insulations [for Rapid Routine Testing Purposes].—Bray, p. 513.
 A Method of Measuring High Insulation Resistances [Loss of Charge Principle with Constant Applied Voltage].—Higgs, p. 513.
 An Apparatus for Measuring the [Radio-] Frequency Spectrum of Sources of Interference with Broadcast Reception.—Wild : Siemens & Halske, p. 272.
 The Measurement of Jonisation Currents by means of an A.C. Bridge and Valve Amplifier.—Ewles, p. 51.
 Theoretical Investigation on Currents through the Bridge and through the Ends of a Lecher Wire System.—Ataka, p. 171.
 Metallic Reflection : Propagation of Electromagnetic Waves along Curved Wires [Experiments on Parity Curved Lecher Wire System].—Eveling, p. 498.
 Uning Discharge hot wave Lucher Wire Sustem.—Interpretered Parity Poils Parity Curved Lecher Wire System].—Eveling, p. 498.
- Curved Wires [Experiments on Partly Curved Lecner wire System].—Eveling, p. 498. Luminous Discharge between Lecher Wires in a partially Evacuated Tube.—Hershberger, Zahl and Golay, p. 498. Method of Measuring the Input Impedance of Ultra-Short-Wave Detectors, and Other Impedances at Ultra-High Frequencies, by a Bridge-Coupled Lecher Wire System.—King, p. 633. The Parallel Wire [Lecher Wire] System as a Measuring Instrument in Short-Wave Technique.—Schmidt, p. 222. Lecher Wire: see also Ultra-Short and under "Propagation of Waves."
- Waves
- The Light Ray as Pointer for Technical Measuring Instruments.— Sieker, p. 223. The Application of Radio to Astronomical Longitude Determinations of the Geodetic Survey of Canada.—Ogilvie, p. 683. Possible Errors in Longitude Determinations depending on the
- Apparent Propagation Velocity of Short Waves.—Stoyko and Jouaust, p. 457. Measurements of the Logarithmic Decrements of Magnetostriction Resonators.—Kopilowitsch, p. 576. High-Frequency Magnetostriction Vibrator [Nickel-Chrome Alloy Rod or Plate].—Matsudaira, p. 109.

- Magnetostriction of a Circularly Magnetised Bar and Its Applications.
- --Mori, p. 50. Method of Determining the Magnetostrictive Constants, and Some Notes on the Motional Impedances of Magnetostrictive Resonators. A -- Aoyagi, p. 633. Hysteresis Phenomena in the Reciprocal Magnetostrictive Effect.
- Kopilowitsch, p. 514. The Joule Magnetostrictive Effect in a Group of Cobalt-Iron Alloys.
- -Williams, p. 109.

Winning, p. 100.
 High-frequency Measurements.—Hund, p. 634.
 Discussion on "The Growth of Electrical Measurement from Its Commencement."—Knowles, p. 51.
 Radioelectric Measurements at the Laboratoire National de Radioélectricité.—p. 633.
 Future Progress in Electrical Measuring Instruments.—Drysdale, p. 683.

- p. 634.
- Mechanical Factor of Merit with respect to Electrical Instruments.-

- p. oor.
 Mechanical Factor of Merit with respect to Electrical Instruments. Goss, p. 401.
 The Partial Elimination of the Averaging Effect ["Smoothing" due to Inertial of Meters.—Gschwind and Lohmann, p. 457.
 Astatic Precision Meters for Current, Voltage and Power.—Siemens & Halske, p. 457.
 Direct-Reading Modulation Meter [using a Detector Valve with nearly Parabolic Characteristic.].—Wada and Goto, p. 513.
 Degree of Modulation measured by Two-Valve Voltmeters, one with Parabolic Characteristic and the other acting as Linear Rectifier.—Wigge, p. 457.
 The Utilisation of Multi-Electrode Vacuum Tubes for Laboratory Measurements.—Ruelle, p. 337.
 Multivibrator with Condensers replaced by Piezoelectric Resonators of Same Natural Frequency and Opposed Temperature Co-efficients.—Telefunken, p. 632.
 Multivibrator Circuit with Two Triodes, or One Tetrode, with Piezoelectric Crystal Replacing a Condenser.—Telefunken, p. 572
- Measurements of the Mutual Impedance of Circuits with Earth
- Return.--Collard, p. 49. The Measurement of Mutual Inductance by the Compensation Method.--Gever, p. 49. Tables for the Calculation of the Mutual Inductance of Any Two
- Coaxial Single-Layer Coils .- Grover, p. 576.

Measurements and Standards.

Measurements and Standards. The Calculation of Mutual Inductances [of Two Coaxial Coils] from the Field Diagram of a Winding.—Potthoff, p. 633. A Null Instrument for A.C. with the Sensitivity of a D.C. Instru-ment.—König, p. 50. The Oersted.—U.S. Bureau of Standards, p. 281. An Oscillator having a Linear Operating Characteristic [and High Frequency Stability].—Arguimbau, p. 211. Theoretical and Experimental Studies on the Frequency Stabilisa-tion of the Dynatron-Type Oscillator.—Hayasi, p. 502. Valve Oscillator with Retroaction through a Rod-Shaped Conductor set in Longitudinal Vibration by Electrostatic Attraction.—

- set in Longitudinal Vibration by Electrostatic Attraction.-
- Runge, p. 170. Study of the Synchronisation of a Self-Excited Oscillator, and of Its Behaviour in the Neighbourhood of Synchronisation.—Subra, p. 619.
- New Radio Test Oscillator [with High Frequency Stability due to "Electron-Coupled" Circuit], p. 457. Checking the Performance of Loop Oscillographs by means of the Cathode Ray Oscillograph.—Loncar, p. 634. Measurement of the Power Output of L.F. Final Stage Amplifiers.— Babite p. 45.
- Babits, p. 45.

- Babits, p. 45. Improvement of the Isochronism of Pendulums by the use of Flastic Stops.—Haag, p. 109. Schuler's Compensating Pendulum [Efficiency, and Accuracy compared with Wireless Time-Signals].—Weber, p. 633. Experiments on the Change of Period of a Blade Pendulum when an Additional Mass-is placed at Different Points, and the Corresponding Theory.—Oosting, p. 109. The Measurement of the Piezoelectric Deformations of Quartz and Tourmain Plates by means of a Modified Ontical Lever Fink
- Tourmalin Plates by means of a Modified Optical Lever .- Fink, p. 171.
- A Piezoelectric Resonator with Uniform Response over a Given Range of Frequencies.—Guerbilsky, p. 508. Thickness Vibration of Piezoelectric Oscillating Crystal.—Koga,

- Initialize Figure 1
 p. 50.
 Vibration of Piezoelectric Oscillating Crystal.—Koga, p. 632.
 A 200-Kilocycle Piezo-Oscillator [for Standard-Frequency Transmissions].—Lapham, p. 632.
 Low-Frequency Mechanical Stimulation of Piezoelectric Crystal to give High-Frequency Oscillations of Natural Frequency of to give High-Frequency Oscillations of Natural Frequency of Crystal—Loewe, p. 171. Method of Altering the Frequency of a Piezoelectric Crystal between
- Fixed electrodes with Air Gap, by Varying the Pressure of the Surrounding Medium.—R.C.A., p. 171. Piezoelectric Control of Oscillator Frequency [Circuit giving Correctly Phased Grid Potential].—Schäffer, Lubszynski and
- Correctly Phased Grid Potential].—Schäffer, Lubszynski and Hoffmann, p. 171.
 Single Frequency Piezoelectric Plate having the Various Diameters proportional to the Square Root of the Modulus of Elasticity in the Corresponding Direction.—Straubel, p. 171.
 Piezoelectric Crystal with Low Temperature Coefficient.—Tele-funken: Osnos, p. 632.
 Piezoelectric Oscillator Circuit with Improved Constancy of Frequency.—Thomson-Houston Company, p. 632.
 Modes of Vibration of Piezoelectric Crystals.—Williams, pp. 171 and 576.

- and 576.

- and 576.
 Temperature Compensation for Piezoelectric Oscillators, p. 109.
 Piezo-: see also Quartz, Rochelle Salt, Tourmalin, and under "Acoustics" and "Miscellaneous."
 Deflections and Vibrations of a Circular Elastic Plate under Tension.—Bickley, p. 333.
 The Use of Triode and Tetrode Valves for the Measurement of Small D.C. Potential Differences.—Hoar, p. 280.
 A Method of Automatic Compensation of Potentials and Its Application to Determining the Potential Distribution in L.F. Electric Fields.—Dunikowski, p. 457.
 Some Important Applications of the A.C. Potentiometer with Capacitive Potential Division [and the Measurement of the Loss Angles of Dielectrics at High Voltages].—Angelini, p. 457.
 The Measurement of the Power Factor and Capacitance of a Con-denser by Comparison with a Mutual Inductance.—Smith, p. 457. p. 457. Some Observations on the Acoustic Field of Piezo-Quartz Crystals.-
- Bücks, p. 333. Some Observations on Oscillating Piezo-Quartz Crystals and their Acoustic Field.—Bücks and Müller, p. 575. Quartz Oscillator with Optical Coupling to Amplifier.—Cady,
- **p. 109.** The Movements of a Quartz Crystal in an Electrostatic Field.
- de Gramont, p. 518. The Different Oscillation Régimes of a Parallelepiped of Quartz
- [and the Cause of Rotation of a Pivoted Crystal].--de Gramont, p. 575.
- Isothermal and Adiabatic Moduli of Elasticity of Quartz Crystals.de Mandrot, p. 171. The Modes of Vibration of Quartz Piezoelectric Plates as Revealed
- by an Interferometer. --Dyc, p. 109. The Temperature Variations of the Frequency of Piezoelectric Oscillations of Quartz. --Gibbs and Thatte, p. 50. Luminous Quartz Resonators as High-Frequency Standards.----Giebe and Scheibe, p. 337.

- The Frequency Variation due to Heat generated by the Vibration of a Quartz Plate: Some Characteristics of a Y-Cut Quartz Plate.—Hatakeyama, p. 50.
 Researches on the Secondary Charges and Mechanical Attractive Forces of a Quartz Crystal Oscillator: the Practicability of Quartz Relays.—Heinrich-Hertz Institute, p. 633.
 Optical Demonstrations of the "Ziehen" [Oscillation-Hysteresis] Effect in a Quartz Crystal Frequency [Controlled Deposition of Silver Electrodes to cure Quartz Crystals ground to Too High a Frequency].—Hunter, p. 223.
 Mounting Quartz Plates [and the Simplification of the Frequency / Temperature Curve by Clamping].—Lack, p. 338.
 Grid/Filament Connection of Quartz in Pierce Oscillator Circuit, superior to Grid/Plate or Plate/Filament Connection.—Macking Number 2014.
- Kinnon, p. 171. A Quartz Plate of Minimum Frequency Variation.—Matsumura and

- A Quartz Flate of Minimum Frequency of X-Cut Rectangular Marzaki, p. 514. Pemperature Coefficient of Frequency of X-Cut Rectangular Quartz Plates.—Matsumura and Kanzaki, p. 514. An X-Ray Examination of the Harmonic Thickness Vibration of Piezoelectric Quartz Plates.—Nishikawa, Sakisaka and Sumoto, 990 p. 338.
- Experimental Determination of the First Piezo-Modulus of Quartz Nussbaumer, p. 50.
- A Triple Interferometer for Distinguishing Flexural and Longi-tudinal Vibrations in Quartz.—Osterberg, p. 223. A Multiple Interferometer for Analysing the Vibrations of a Quartz
- Plate.—Osterberg, p. 457. The Researches of the late Dr. D. W. Dye on the Vibrations of
- Quartz [including his Ring Oscillator].—Rayner: Dye, pp. 338 and 514.
- Variation of Dielectric Constant of Quartz with Applied Potential [and with Temperature].—Saegusa and Nakamura, p. 280. On the Variation of the Electrical Conductivity of Quartz, Tridymite, and Cristobalite with Temperature.—Shimizu, p. 514. A Simple Method of Determining the First Piezo-Modulus of Quartz from Measurements of a Quartz Resonator.—Székely,
- p. 50.
- Quartz Crystal and Thermostat in Bulb .- Telefunken : Bechmann, p. 280.
- p. 230.
 Temperature Variation of Viscosity and of the Piezoelectric Constant of Quartz.—Van Dyke, p. 171.
 Measuring the Temperature of a Quartz Oscillator Crystal in Its Bulb, p. 109.
 Discussion on "The Campbell-Shackelton Shielded Ratio Box."—
- Behr and Williams, p. 51. Measurement of the Internal Resistance of B-Amplifier Valves [by a Modified Wheatstone Bridge Method].—Babits and Szalontay, p. 634.
- The B.A. Standards of Resistance, 1865-1932 .- Glazebrook and
- Hartshorn, p. 51. Hartshorn, p. 51. Two Simple Methods of Absolute Measurement of Electrical Resistance in Terms of Inductance and Frequency.—Nettleton and Balls, p. 513.
- First Comparisons of the National Standards of Electrical Resistance, carried out at the International Bureau of Weights and Measurements.—Pérard and Romanowski, p. 576. Methods for Measurement of High Resistance at High Frequency.—

- Methods for Measurement of right Resistance at right Arequisity. Taylor, p. 171. The Converse Piezoelectric Effect in Mixed Crystals Isomorphous with Rochelle Salt.—Bloomenthal, p. 575. On the Determination of Some of the Elastic Constants of Rochelle Salt by a Dynamical Method.—Davies, p. 576. Electrical Properties of Isomorphous Crystals of Rochelle Salt and Scidium Tartate —Bremeiw and Kurtschatow.
- Sodium Ammonium Tartrate .-- Eremejew and Kurtschatow, p. 575.
- The Natural Frequencies of Rochelle-Salt Bar Oscillators : Un-expected Departure from Usual Formulae.—Heinrich-Hertz
- Institute p. 633. The Lower Curie Point in Rochelle Salt.—Kurtschatow, p. 576. Experimental Investigations on the Piezoelectric and Dielectric Properties of Rochelle Salt.—Schwartz, p. 164. A New Method of Determining the Statical Dielectric Constant
- A New Method of Determining the Statical Dielectric Constant of Semiconductors and Measurements of the Dielectric Constant of Rochelle Salt.—Oplatka, p. 401.
 High-Frequency Measuring Apparatus and Signal Generators.— Siemens & Halske, p. 48.
 Skin Effect in a Stratified Cylinder of Circular Section.—Fischer and Strutt p. 578
- Strutt, p. 576.
- The Measurement of Small Electrodynamic Forces with the Condenser Microphone.—Agricola, p. 223. New National Radio Standards [for Broadcast Receivers and

- New National Kadio Standards for Broadcast Receivers and Components], p. 110. Apparatus for the Comparison of the Electromotive Forces of Standard Cells.—Vigoureux : Brooks, p. 634. The Wireless World Direct Reading Station Finder.—Smith, p. 223. Frequency Requirements and the Control of Frequency for Syn-chronous Motor Operation of Astronomical Telescopes.—Moffitt,
- p. 49. Set Analysers [for Testing Broadcast Receivers].—Lewis, p. 401.

E

Measurements and Standards.

Characteristics of Thermo-Ammeters for use at Radio Frequencies. -Takaya, p. 280. A New Way of Making Use of Thermoelectric Phenomena.—Égal,

- A New way to interest of peak Values of Alternating Currents and Voltages by means of a **Thyratron** [using the Relationship between Grid Voltage and Minimum Striking Voltage on Anode]. Hughes, p. 513. Robot Clock announces Time from the Paris Observatory.—Esclan-
- gon, p. 576.
- Automatic Equipment for the Transmission of the Exact Time over the Telephone System, p. 223. Further Results in the Study of Apparent Variations of the Vertical
- with the Hour-Angle of the Moon [and the Variation in Time-Determinations at Greenwich and Washington with Lunar Hour-Angle and Declination].—Stetson : Loomis and Stetson, p. 633

- Time-Keeping-Old and New.-Hope-Jones, p. 223. Synchronous Electric Time Service.-Warren, p. 109. Studies of the Transmission of Time Signals [and the Determination of Delay Times].—Jouaust, p. 515. On the Piezoelectric Properties of Tourmalin.—Fox and Underwood,
- p. 338.
- Discussion on Overtones in Tourmalin-Crystal Vibrations .- Heinrich-Hertz Institute, p. 632. Relations between Etch Figures and Piezoelectric Properties of

- rich-Hertz Institute, p. 682.
 Relations between Etch Figures and Piezoelectric Properties of Tourmalin.—Matsumura and Goto, p. 514.
 Effect of Temperature upon Piezoelectric Vibration of Tourmalin Plates.—Matsumura, Ishikawa and Goto, p. 514.
 Longitudinal and Flexural Vibrations of Tourmalin Plates.—Peträlika, p. 223.
 Short Wave Circuit emitting Trains of Waves at Equal Intervals of Tomesers].—Petrucci, p. 391.
 The Measurement of the Power of a Transmitter by Incandescent Lamp and Photronic Cell.—Houldson, p. 337.
 A New "Compensator" Measuring Equipment for the Determination of the Transmission Equivalent of Quadripoles [and Amplifiers].—Piesch, p. 513.
 Attenuation of Transmission Lines : Simple Method of Measuring.—Strutt, p. 327.
 Method of Field-Strength Measurement, especially for Ultra-High Frequencies.—Sohnemann, p. 279.
 The Measurement of [Ultra-] High Frequency Potentials with the Thread Electrometer.—Ultra-Radio [Ultra-Short] Waves [using Special Lecher Wire System].—Hoag, p. 222.
 Wavelength Measurement on Ultra-Short Waves [Use of Small Incandescent Lamp in Tuned Circuit, with Tourmalin Crystal in Parallel].—Leithäuser and Petrilka, p. 109.
 On Standards for Measurement of Ultra-Short Waves.—Leithäuser and Petrilka, p. 223.

- and Petr ilka, p. 223. Tourmalin Resonators for Short and Ultra-Short Waves .- Petržilka,
- p. 108.

p. 108.
New Method of Measuring Electric and Magnetic Properties of Metals in the Region of Ultra-Short Electromagnetic Waves.— Potapenko and Sanger, p. 279.
Practical Measurement of Ultra-Short Waves.—Whitehead, p. 456.
Ultra-High and Ultra-Short : see also Electrometer, Lecher Wire.
A New System of Electric and Magnetic Units, and Their Dimensions.—Bucher, p. 456.
International Action on Units in Electricity and Light.—Bureau of Standards, p. 456.
Three Superfluous Systems of Electromagnetic Units.—Campbell, p. 280.

- Dimensions of Fundamental Units.—Denton, p. 456. Two Significant Comparisons of the Use of the Absolute Unit M.K.S. (and of the orthodox C.G.S. Unit : Calculations of the Capacity of the Earth and the Inductance of a Coil].—Giorgi, p. 456.
- Electric and Magnetic Units. The Basis of a System of Definitions.

- Electric and Magnetic Units. The Basis of a System of Definitions. —Glazebrook, p. 338. Electrical and Magnetic Units.—Griffiths, p. 280. Conference of the Symbols, Units and Nomenclature Commission of the International Union of Pure and Applied Physics, and Its Results.—Kennelly, p. 280. A New System of Units in Electromagnetism.—Verschaffelt, p. 51. Suggested Unit of Vibration Amplitude [the "Pal," corresponding to the Phon in Acoustics].—Zeller, p. 401. Methods of Measuring Voltage, Current and Power in Pulsating Current.—Okitsu, p. 634.

- Correction of Frequency Error in Moving Iron Voltmeters .-- Gall :
- Carter, p. 172. Correction of Frequency Error in Moving-Iron Voltmeters.—Camp-bell: Carter : Gali, pp. 50 and 280. New Type of Electrostatic Voltmeter [for measuring Potential Gradients and High Electrostatic and R. F. Voltages].—Field, pp. 179 and 824
- pp. 172 and 634. A Rotary Voltmeter.-Kirkpatrick, pp. 50 and 172.

- A Valve-Voltmeter for Measurements of Hydrogen-Ion Concentration.—McFarlane, p. 401.
 Application of Compensated Valve-Voltmeter to Measurements of Glass Electrode Potentials [without Use of "Electrometer" Valves].—McFarlane, p. 575.
 A Survey of the Vacuum-Tube Voltmeter Field.—Nason, p. 401.
 Valve Voltmeters.—Payne, p. 634.
 A Thermionic Voltmeter with Logarithmic Calibration Curve [particularly for Acoustic Measurements].—Rommel, p. 50.
 An Amplifying Voltmeter [using a Two-Grid Valve to generate A.F. Current with Amplitude depending on D.C. Voltage to be measured : Milliammeter reads Changes of 2 × 10⁻³ Volt].—Roulleau, p. 513.
 A Multi-Range Mains-Operated Valve Voltmeter,—Smvth : G.E.C.,
- A Multi-Range Mains-Operated Valve Voltmeter .--- Smyth : G.E.C. , p. 337.
- An Improvement in Vacuum Tube Voltmeters [for Audio-fre-
- quencies].—Somers, p. 280. A Valve Wattmeter.—Mallett, p. 634. A New Apparatus for Determining the Relationship between Wavelengths of Light and the Fundamental Standards of Length. -Sears and Barrell, p. 49. On the Beat Method of Calibrating Wavemeters [Liability to 0.5%]
- Error].—Kahan, p. 400. Contribution to the Study of the Stability of Oscillations in Coupled Circuits [e.g. in Oscillating Circuit coupled to Wavemeter].— Contribution to the study of the drawing of the Wavemeter].— Circuits [e.g. in Oscillating Circuit coupled to Wavemeter].— Mercier, p. 443. A Wavemeter with Alternative Close and Open Scales.—Radio Research Station, p. 456. Interference Wavemeter with Large Wave Range for Laboratory Use.—Rohde and Schwarz, p. 49. The Temperature Coefficient of the Saturated Weston Cell.—Vigon-reux and Watts, p. 280.

SUBSIDIARY APPARATUS AND MATERIALS

Plateless Batteries [Accumulators] .- Block Batteries Ltd. : Fuller,

p. 281. An Important Improvement in the Construction of the Lead Accumulator [the Féry-Carbone Non-Sulphating Cell], p. 459. Iodine Accumulators.—Fourcault: Boissier, p. 282. Electrical Accumulators according to Recent Patents.—Jumau,

p. 341.

Halogen Salts Accumulators .- Reyval : Jumau, p. 282,

- Accumulators : see also Storage. Magnetic Properties and Chemical Linkage in Alloys.—Dorfman,

- Magnetic Properties and Chemical Linkage in Alloys.—Dortman, p. 578.
 The Use of Two-Grid Valves for the Amplification of Continuous Currents.—Donzelot and Divoux, p. 460; see also Amplifier.
 The Elimination of Background "Noise" in Sensitive Pulse Amplifiers.—Curtiss, p. 282.
 A Resistance-Coupled [Two-Stage] Amplifier for Measuring Ionisation Currents.—Curtiss, p. 579.
 Method of Compensating the Plate Currents [in a Triode Amplifier to allow the use of a Sensitive Instrument].—Donzelot and Divoux, p. 113.

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- Campbell, p. 636. A Direct Current Amplifier.—Macdonald and Macpherson,
- Campbell, p. 638. A Direct Current Amplifier.—Macdonald and Macpherson, p. 228. Operating Constants for Direct-Current Thermionic Amplifiers.— Macdonald and Tweed, p. 516. A High-Gain A.C. D.C. Amplifier [Pentode as Plate-Circuit Resistance].—Meissner, p. 638. A Supersensitive Amplifier for Measuring Small Currents.—Moles : G.E.C., p. 341. On Transients in Transformer Amplifiers.—Nowotny, p. 340. The Audio Transformer as a Selective Amplifier.—Pawley, p. 218. A Direct Current Amplifier With Good Operating Characteristics [using Radiotron Valves].—Taylor and Kerr, p. 228. A Direct current Amplifier Circuit.—Turner, p. 516. Shot Effect and Thermal Noise in the Photocell Amplifier.—von Optim. p. 334.

- Orbán, p. 334. The Application of a Thermionic Amplifier to the Photometry of the Stars.-Whitford, p. 223.
- Stars.--Whitford, p. 223.
 A New Method for Amplifying and Recording Small E.M.Fs [using a Photoelectric Cell].--Morgan, De Vore and Baker, p. 636.
 A Simple Method of Analysing Strip Records of Registering Apparatus.-Dalchau, p. 285.
 A New Method of Frequency Analysis applicable to Acoustic and Radio Frequencies.--Fehr and Kreielsheimer, p. 578.
 A Mechanical Aid to the Analysis of Complex Spectra.--Harrison, r. 998.
- p. 228.

- The Resonance Method of Wave-Form Analysis [and a Résumé
- of Other Methods).--Morgan, p. 113, Analysis : see also Harmonic, and under "Acoustics." On the Sparking Condition of Low Voltage Arcs and Grid-Controlled Low Voltage Arcs [Thyratrons]. I.--Klaiber, p. 577, A Geometrical Method of Integration and an Apparatus for Measur-

- A Geometrical Method of Integration and an Apparatus for Measur-ing the Areas of Curved Surfaces.—Myard, p. 638. The Automatic Transmission by Radiotelegraphy of the Reading of an Instrument by Two Audio-frequency Modulations of Varying Depth.—Csejkovits and Dieckmann, p. 460. The Electrical Conductivity of Uranium Dioxide and Its Use as Series Resistance, especially for Iron-in-Hydrogen [Barretter] Resistances.—Meyer, p. 284. Stabilised "B" Supply for A.C. Receivers [using Commercial Neon Glow Lamps].—Dekker and Keeman, p. 112. The Breakdown Voltage of Luminous_Nitrogen_Tubes with Variable Electrode Distance. I. Straight Tube.—Fricke, p. 284.
- p. 284.
- Is the Breakdown of Insulating Liquids a Heat Process ?- Koppelmann, p. 578. A New Method of Eliminating Edge Effect in Electric Breakdown.
- -Norcross, p: 637. The Mechanism of the Electrical Breakdown of Transformer Oil-
- Rebhan, p. 341. The Influence of the Steepness of Rise of A.C. Voltage on the
- Breakdown Potentials of the Rare Gases and Air in Luminous Tubes.—Spielhagen, p. 284. The Oscillographic Investigation of the Breakdown Process due
- to Overheating [in a Solid Dielectric]—von Philippoff, p. 341. A Study of the Electrical Breakdown of Liquids [Paraffin Oil and Xylo]] by Means of the Electro-Optical Shutter.—Washburn, p. 341.

- An Electrical Calculating Machine.—Mallock, p. 460. A Calculating Rule of Highly Elastic Rubber, p. 579. H.T. for the Car Set.—Dinsdale, p. 459. Barrier Layer Investigations on Carborundum Crystals.—Claus, p. 53.
- p. 635.
 A Cold-Cathode Oscillographs.—Kroemer,
 p. 635.
 A Cold-Cathode Oscillograph for Low Excitation Voltage.—Rogow-
- A control and Malsch, p. 283. Applications of the Cathode-Ray Oscillograph [Factors affecting Accuracy of Measurements, and Their Compensation : Oscillo-graph with Magnetic Deflection].—Batcher, p. 224. Cathode Ray Oscillography.—Bedford, p. 283.
- A New Multiple Cathode-Ray Oscillograph.-Boekels and Dicks, p. 283.
- Simultaneous Traces with Cathode-Ray Oscillograph [with Single Ray: the Use of a Synchronised Rotary Switch].—Bradner Brown, p. 578.
- The Optics of the Braun Low-Voltage [Cathode-Ray] Tube .- Brüche, p. 458.
- p. 498.
 The Use of the A.C.-Driven Cathode-Ray Tube as Synchronoscope. —Brüche, p. 635.
 The Technique of the High-Speed Cathode-Ray Oscillograph.— Burch and Whelpton, pp. 51 and 339.
 Comparison of Electronic and Optical Blackening with the Cathode Ray Oscillograph.—Buss and Pernick, p. 52.
 Cathode Ray Photography of Random Electrical Transients.— Chapman, p. 408.

- Chapman, p. 403. New [Low-Voltage] Cathode-Ray Oscillograph.—Dantscher: A
- AEG. p. 635.
- Use of Cathode-Ray Oscillograph for obtaining Frequency-Response Curves.—Davis, p. 570. The Limiting Efficiency of the Cathode-Ray Oscillograph with Lens

- The Limiting Efficiency of the Cathode-Ray Oscillograph with Lens Recording.—Dodds, p. 517. The Recording of Surges [Simple Equipments as Substitutes for the Cathode-Ray Oscillograph].—Dodds and Fucks, p. 635. Recent Developments in Cathode-Ray Tubes and Associated Apparatus [including Cathautograph and Cathode-Ray Com-pass].—Du Mont, p. 458. New Cathode-Ray Tube Screen Material.—Du Mont Laboratories, n. 458.
- p. 458.
- A Simple Circuit with Compulsory Coupling of the Beam-Locking Device and the Time Deviation in the Cathode-Ray Oscillograph. -Fucks and Kroemer, pp. 283 and 635. Some Experiments on the Electrostatic Concentration of Cathode

- Some Experiments on the Electrostatic Concentration of Cathode Rays.—Graupner, p. 51.
 The Cathode-Ray Oscillograph in Radio Research.—G. W. O. H.: Watson Watt, Herd and Bainbridge-Bell, p. 516.
 A Linear Timing Axis for Cathode-Ray Oscillographs [using "Westinghouse Industrial Tube"].—Haller, p. 635.
 A Method of Extending the Frequency Range of the Cathode-Ray Tube.—Hartridge, p. 172.
 On Experience with the Use of Bromide Paper for [Internal] Cathode-Ray Oscillograms.—Hayakawa and Hishiyama, p. 517.
 The Sensitivity of the Braun [Cathode-Ray] Tube with Gas Concentration, at Various Frequencies [0 to 1 Megacycle/Sec.].— Heimann, p. 51 : see also below (von Ardenne).
 The Use of the Cathode-Ray Oscillograph at Ultra-High Frequencies. —Hollmann, p. 634.
- -Hollmann, p. 634.

- Cathode-Ray Oscillograph for Ultra-High-Frequency (B.-K.) Oscillations: Electron Path-Time Error Automatically Com-pensated.—Hollmann: von Ardenne, p. 111.
 Stroboscopic Investigations with the Cathode-Ray Oscillograph.— Hollmann and Saraga, p. 282.
 A Cathode-Ray Oscillograph for Internal Recording and Rapid Changing of Film without Breaking the Vacuum.—Holzer and Knoll, p. 51.
 Distortions due to Space Charge in Cathode-Ray Tubes.—Hudec, p. 453.
- p. 453. Intensity Control of the Gas-Concentrated Cathode-Ray by Wehnelt

- The Electron Current Density in Cathode-Ray Discharge Tupes.— Malsch, p. 635. A Cathode-Ray Oscillograph for Direct Photography of Very High Direct and Alternating Voltages.—Messner, p. 458. Intensity Control of Gas-Concentrated Cathode-Rays by Electrical Fields—Wehnelt Cylinder.—Michelssen and Kleen, pp. 105-106. Lightning Transients—Measurement by Cathode-Ray Oscillograph [Ferranti Model].—Miller, p. 111. Cathode-Ray Tubes Costing 75 to 150 Marks.—Pressler Company, m. 300-400
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 Time-Marking a Cathode-Ray Oscillograph [by Unfocusing the Spot by applying a Periodically Varying Potential to the Wehnelt Cylinder].—Richardson, p. 283.
 Sensitive Cold Cathode-Ray Oscillograph.—Rogoswki, p. 402.
 Cathode-Ray Oscillograph, Survey of Cold-Cathode Oscillograph Developments].—Rogowski, p. 516.
 Note on the Cathode-Ray Oscillograph.—Rogoswki, p. 635.
 The Possibility of Focusing Cathode-Ray Beams of Large Initial Cross-Section.—Ruska, p. 517.
 Wave-Form Studies with the Cathode-Ray Oscillograph [with Description of General Radio Tube and Controlled Linear Sweep Circuit].—Soott, p. 51.
 The Simultaneous Recording of Several Processes with the Cathode-Ray Oscillograph [using an Ordinary Single Tube].—Sewig, p. 339.
 High-Speed Cathode-Ray Oscillographic Recording on Computer 1.

- p. 339.
 High-Speed Cathode-Ray Oscillographic Recording on Commercial Photographic Paper.—Stekolnikoff; Förster, p. 458.
 Cathode-Ray Tubes [Two New Gas-Focused Types].—Sutherlin and Harcher, p. 111.
 Study of H.T. Circuit Breakers, using a Cathode-Ray Oscillograph with Film wound on Rotating Drum.—Van Sickle and Berkey, p. 635. p. 635.

- von Ardenne, p. 578. Cathode-Ray Oscillography (Physical Society Discourse).—Watson Watt, pp. 172 and 224.
- Watt, pp. 172 and 224.
 Applications of the Cathode Ray Oscillograph in Radio Research.
 Watson Watt, Herd and Bainbridge-Bell, p. 402 : see also above (G.W.O.H.).
 Cathode-Ray : see also Electron, Pliotrons, Wehnelt, and under "Phototelegraphy and Television."
- Design of an Apparatus for Cathode Sputtering .- Darbyshire,
- Design of an Apparatus for Calculate Determined p. 341. The Calculation of Iron-Cored Chokes [for Telephonic Frequencies]. --Maroochi, p. 226. See also Iron-Cored. The Analysis of Processes occurring in Very Short Times [by High-Speed Chematography up to 80 000 Pictures per Second].-Ende, --Ende, --Ender 2006. pp. 112 and 225.

pp. 112 and 223. Cinematography : see also Discharge. The Influence of a Metallic Cover on the Losses, Inductance and External Field of a Coll.—Kaden, p. 576. Design of Radio-Frequency Coils.—Place, p. 341. Special Design of H.F. Coilg [for Master-Oscillator] to give Constant Linducture over Terrenet Research 408 C. Line Covierence

- Inductance over Temperature Range of 40° C .-- Ure, Grainger
- and Cantelo, p. 480. Note on a New Rotating Commutator [for Charging Condensers, etc.].—Telang, p. 285. The Essentials of Wireless Components. Part I: High-Frequency
- Chokes.-Scroggie, p. 577.
- Cost versus Quality in Radio Set Components [I.R.E. Symposium], p. 638.
- The Measurement of the Capacity of Commercial Electrolytic Condensers, and an Investigation of Its Dependence on Tempera-ture, Voltage and Prolonged Loading.—Bauder and Jannsen,

- ture, Voltage and Prolonged Loading.—Bauder and Jannsen, p. 112. A Plate Condenser with Negative Capacity.—Benndorf, p. 460. Electrolytic Condensers.—Coursey, p. 173. Capacitance and Potential Gradients of Eccentric Cylindrical Condensers.—Dawes, p. 340. Conductivity and Loss Angle Measurements on Paper Condensers for 50-Cycle Supply with Superposed High Frequency.—Febr and Hubmann n. 632 and Hubmann, p. 637.

- A.C. Capacities of Electrolytic Condensers, and Potential Gradients
- A.C. Capacities of Electrolytic Condensers, and Potential Gradients in Anodic Films.—Godsey, p. 402.
 Note on Thermal Instability in Cylindrical Condensers due to Dielectric Losses [Calculation of Electric Intensity giving In-stability].—Goodlet, p. 577.
 Gang Condensers of Variable Capacity for Modern Receivers [in-cluding the Problem of "Microphonics"].—Koepping, p. 112.
 The Inductive Resistance of Roll-Type Condensers at High Fre-quencies.—Kotowski and Kühn, p. 340.

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- p. 460. VDE Test Specifications for Condensers for Broadcast Receivers and
- Interference Prevention, p. 227. Balancing Device for Rotating Condensers, etc., by Separately Screw-Adjusted Segments of a Slotted Stator Plate.—von
- Screw-Adjusted Segments of a Slotted Stator Flate.—von Kramolin, p. 638. Air-Type Alignment Condensers for Plug-In Coils [replacing Mica-Type "Trimmers"], p. 516. The Influence of Surface Charges on Measurements of the Con-ductivity of Poor Conductors.—Goldhammer, p. 637. New Connecting Leads for Broadcast Receiver Equipments.—

- New Connecting Leads for Broadcast Receiver Equipments.— AEG, p. 637.
 Constant Direct Current [by use of Grid-Controlled Rectifier: Drop of Main Rectified Current in Iron-Wire Ballast Lamp used as Grid Bias].—Westendorp, p. 341.
 Measurements on Contact Potential Difference between Different Faces of Copper Single Crystals.—Farnsworth and Rose, p. 402.
 Elmet Metals ["Rotung" and "Silvung".—Specially Prepared Tungsten with Copper and with Silver: for Contacts and Therm-ionic Valves], p. 637.
 Converters : see also Gas-Filled, Inverters, Rectifiers.
 Compressed Powder Vores [for Pupin Coils, etc.].—Deutschmann, n. 113.

- p. 113.
- Iron-Content Cores for High-Frequency Coils [Vogt Iron (Ferrocart)].
- -Schneider, p. 403. A Mercury Jig for Testing [Permeability of] Toroidal Cores [of Permaloy-Dust].--Young, p. 403. Controlled Silent [Corona] Discharge at Atmospheric Pressure.-
- Gemant, p. 401. A Recording Frequency Counter depending on the Time Constant
- A Recording Frequency Counter for Atmospherics, Tachometer, etc.].— Lugeon and Gurtzman, p. 457.
 A Circuit for Recording Multiply-Coincident Discharges of Geiger-Müller Counters.—Johnson and Street, p. 341.
 A New Coupling for Electric Drive, with Overload Release.—AEG,
- p. 579.
- A new couping for Electric Drive, with Overload Release.—AEG, p. 579.
 A.C. Rectification by Photosensitive Aggregates [Objections to Eccles's Thermo-electric Theory of Crystal Detector: New Theory].—Barnard: Eccles, p. 402.
 A New Detector [Insensitive Galena Crystal treated with Sulphur, with Copper Electrode].—Cayrel, p. 459.
 A Note on the Magnetic Susceptibilities of Cuprous Oxide Films.—Bhatnagar and Mitra, p. 515.
 Electrical Conductivity of Cuprous Oxide [and Its Variation with Temperature: Energy of Electron Dissociation].—Jusé and Kurtschatow, p. 402.
 On the Optical Transparency of Cuprous Oxide in Connection with the Electrical Conductivity.—Mönch, p. 53.
 Thermo- and Voltaic E.M.F. of Cuprous Oxide,—Mönch, p. 515.
 On Thermal and Voltaic E.M.Fs of Curpous Oxide.—Mönch and Stechhöfer, p. 636.
 Cuprous Oxide : see also Rectifiers.
 An Apparatus for Tracing the Mean Derivative of a Function represented by Its Curre in Cartesian Co-ordinates, p. 517.
 Curve Plotter and Comparator for Laboratory and Production Test Uses.—Isler, p. 228.
 Deetibel and Decineper Charts [for Simplifying Calculations of Power Gain and Loss in Transmission Lines and Radio Amplifiers].—Sklar, p. 517.

- Gain and Loss in Transmission Lines and Radio Amplifiers].— Sklar, p. 517.
 Electro-Mechanical Determinant Machine.—Weygandt, p. 579.
 Commercial Testing of Solid Dielectrics [Survey of Methods in Various Countries].—Caviglia, p. 227.
 Contact Phenomena in Dielectrics.—Electrical Research Associa-tion : Metropolitan-Vickers Company, p. 340.
 Commercial Dielectrics : the Factors concerned in Their Dielectric Losses : Electro-Osmotic Mechanism, and Semi-Permeability : Intense Polarisation retained by a Dielectric solidified in an Electric Field : etc.—Lahousse, p. 546.
 Some Observations of Residual Charge in Dielectrics.—McCleery, p. 341.
- p. 341.
- (three).

- The Dielectric Losses in Impregnated Paper.—Whitehead, p. 340. Calculation of the Dielectric Constant of a Salt from a Single Measurement of a Mixture of Air and the Salt .- D. A. G. Bruggeman,
- p. 637. On the Bearing of the Natural Infra-Red Oscillations of Materials
- on their Dielectric Losses.—Czerny and Schottky, p. 31. Dielectric : see also under "Propagation of Waves." Study in the Discharge in an Ionic Tube with the help of a Cinemato-
- graphic Apparatus.—Dolejsek and Dråb, p. 224. The Possibility of Introducing Very High Potentials into Discharge **Tubes** [2 130 kv, by Long Sub-divided Path with Magnetic Fields at the Bends].—Sitnikov, p. 52. The Tuning Curves of Electrical Distant Control Elements.—Scha-
- dow, p. 53.
- S.F.R. Chauveau Auto-Alarm [Distress Signal] Receiver, p. 638.
- A Drawing Instrument for Large Radius Arcs.—Simeon, Tests on the Performance of Dry Cells.—Ruelle, p. 226. -Simeon, p. 460.
- Dry Cells : see also Primary
- Dry Cells : see also Primary. Dynamos for Radio Transmitting Stations.—Hutt: Brown-Boveri Company, p. 459. A Voltage-Multiplying Connection for Influence Electrical Machines and a Model giving 210 kv for Insulator Testing, etc.—Hoch-häusler, p. 687. A Compact [Oil-Cooled] Electromagnet for General Purposes [giving 32 500 Gauss].—Bates and Lloyd-Evans, p. 578. An Improved Balanced Circuit for Use with Electrometer Tubes.— Turner and Siegelin, p. 636. The Application of the Electrometer Triode to the Measurement of Ionisation Current.—Teegan and Haves, p. 403.

- The Application of the Electrometer Triode to the Measurement of Ionisation Current.—Teegan and Hayes, p. 403.
 Electrometer Triode in the X-Ray Ionisation Spectrometer.— Wooster: Robinson, p. 403.
 The Trajectories of Electrons in a Longitudinal Magnetic Field.— Kwal, p. 283.
 On the Paths of Electrons in an Electric and Magnetic Field with Axial Symmetry [Theoretical Paper].—Störmer, p. 339.
 Flexible Electron Beams.—Brüche, p. 51.
 The Geometry of the Accelerating Field as It Affects the Electron Beam with Gas Concentration.—Brüche, p. 53.
 Electron Beam and Gas Discharge.—Brüche, p. 283.
 Remark on the Space-Charge Field of the Gas-Concentrated Electron Beam, --Engel, p. 115.
 On the Formation of Images by Electron Beams on the Lines of Geometrical Optics.—Glaser, p. 283.

- The Dependence of Electron Beam Concentration on the Kind of Gas.—Richter, p. 517. On the Explanation of the Gas-Concentrated Electron Beam.—
- Rogowski and Graupner, p. 111. Theory of the Gas Concentration of Electron Beams.-
- -Scherzer, p. 458. The Electric Electron Condensing Lens.—Johannson and Scherzer,
- p. 224.
- Electron Lenses.--Davisson and Calbick, p. 224.

- p. 224.
 Cinematograph Records of Oxide Cathodes using an Electron Microscope.—Briche and Johannson, p. 111.
 Some New Cathode Investigations with the Electrical Electron Microscope.—Briche and Johannson, p. 111.
 Observations of a Barium Cathode, sputtered on Nickel, with an Electron Microscope.—Briche and Johannson, p. 111.
 Observations of a Barium Cathode, sputtered on Nickel, with an Electron Microscope.—Briche and Johannson, p. 578.
 Theory of the Electron Microscope...Classer, p. 517.
 The Electron Microscope.—Knoll and Ruska, p. 51.
 The Geometrical-Optical Portrayal of Hot Cathodes by Electron Microscope].—Knoll, Houtermans and Schulze, p. 283.
 Formation of Images by Secondary Electrons in an Electron Microscope...-Rosener, p. 283.
 On the Theory of the Electron Microscope...-Posener, p. 283.
 Formation by the Electron Microscope...-Posener, p. 283.
 The Delineation of Irradiated Films in the Electron Microscope...-von Borries and Ruska, p. 517.

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- Picht, p. 224. On the Theory of Electron Optics.—Picht : Scherzer, p. 458. The Theory of the Lens Errors in Electron Optics.—Scherzer, p. 244. On Electron. Optics. [Survey of the Focusing of Electron Beams].—
- Zworykin, p. 578
- Self-Focusing Electron Streams [e.g. in Cathode-Ray Tubes].-Bennett, p. 635.
- The Cathautograph: an Electronic Pencil [using a Fluorescent Screen with a Decay Period of about 30 Seconds].--Du Mont, p. 224. Class "B" Eliminator [using special Neon Tube Stabiliser].—Page,
- p. 341.

- Damping Measurements on Iron-Cored [Ferrocart] Coils.-Frühauf, p. 172.
- p. 172. Iron Powder Compound Cores for Coils [Ferrocart, etc.].— G.W.O.H., p. 173. How Ferrocart is Made.—Schneider, p. 281. Ferrocart Schneider, p. 281.
- Ferrocart.—Schneider, p. 515. "After-Effect" Losses in Ferromagnetic Materials for Weak Alternating Fields.—Goldschmidt, p. 112. Comparison between Cascades ot Tuned R. F. Amplifiers and the
- Band-Pass Filters of Cauer and of Jaumann .- Baerwald,
- p. 516. The Properties and Calculation of the Multiple Bridge Filter.
- Cauer : Jaumann, p. 228. Critical Reviews of Books and Papers on Electric Filters.—David,
- p. 443. A Recent Contribution to the Design of Electric Filter Networks
- [Cauer's Method in Simplified Form of Sufficient Accuracy for Most Cases].—Guillemin : Cauer, p. 52. A Filter for an X-Ray Power Supply [Greinacher Rectifier Circuit and Balanced Pi-Type Low-Pass Filter].—Hoag and Andrew,
- p. 225. A Filter for the Intermediate-Frequency Amplifier [of a Super-
- The for the intermediate-Frequency Amplifier for a Super-heterodyne Receiver].—Piecok, pp. 211-212.
 The Construction and Balancing of Intermediate-Frequency Band-Pass Filters.—Sturm, p. 638.
 Filters: see also under "Reception," "Acoustics and Audio-Frequencies."
- The Efficiency of Fluorescence of Sodium Salicylate .- Doubouloz,
- p. 458. The Variation of the Intensity of Fluorescence with the Wavelength of the Exciting Radiation [and the Effect of the Solvent].—
- Pabrikart, p. 578. Quantitative Study of the Inhibiting Action of Certain Ions on the Fluorescent Power of Uranine [the Sodium Salt of Fluorescein].— Bouchard, p. 284.
- A Spectroscopic Method of Determining the Excitation of Lumines-cence. [for the Rapid Choice of the Ultra-Violet Wavelength suitable for Various Fluorescent Substances].-Heyne and Pirani, p. 225.
- p. 220.
 The Spurious Ring exhibited by Fluorescent Screens.—Hughes, p. 517.
 A Simplified Frequency-Dividing Circuit [using One Pentode Valve: for Frequency-Measuring Equipments].—Andrew, p. 578.

- p. 576.
 Taylor's Frequency Tripler [Explanation of Action].—Pillai and Mowdawalla, p. 515.
 "Wax-Operated Switches" and Metallised Wax Strips as Fuses for Instruments, Fractional-H.P. Motors, etc.—Bullen, p. 578.
 Fusible Jack for Multi-Range Meters [each Jack containing the Appropriate "Littel-fuse" and secured under the Binding Post of One Rangel ____ 925.
- Appropriate Little fuel that the Grid Control of Gas-Discharge Tubes [including Mercury-Vapour Rectifiers with Grids].--Glaser, p. 111. The Mode of Action of Gas-Discharge D.C. Converters.—Laub,

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- p. 339. The Ignition Process and Power to the Grid in Hot-Cathode Gas-Filled Relays [Thyratrons, etc.].—Klemperer and Steenbeck, p. 636.
- Gaseous Discharge Tubes for Radio Receiver Use [as Visual Tuning Indicator with or without "Noise Gate"].—Dreyer : Senauke,
- p. 272. The Dielectric Losses of Glass and Their Dependence on Its Composition.—Keller, p. 282. The Dielectric Strength of Thin Layers of Glass and Mica.—Alexan-
- drow and Joffe, p. 637. The Control and Extinction of a Glow Discharge in a Tube with Mains-supplied Cathode and a Third Electrode.—Badareu,
- A Unipolar Form of "Gliding Corona" [a Kind of Glow Discharge; and a Criticism of Gemant's "Electrophotography" of the Porous Structure of Insulating Materials].—Coehn and Ziegler,
- Polous Structure 1 p. 577. The Theory of Glow-Discharge Valve Tubes [for Protecting Devices : Possibility of Using Greater Electrode Gaps].—Heer, p. 578. The Heavy-Current Glow Discharge at Atmospheric Pressure : A New Type of Discharge.—Heer and Thoma : Krug, pp. 112 and one
- A free Type of Establishing and 228. The "Stabilisator" [Glow-Discharge Potential Divider and Voltage Regulator].—Körös, p. 228.

- The Provision of Several Different Anode Voltages by the "Stabili-volt" Glow-Discharge Tube .-- Körös, p. 577.
- The Provision of Several Different Anode Voltages by the "Stabin-volt" Glow-Discharge Tube.-Körös, p. 577. A New "Amplitude-Limiting" Glow-Discharge Lamp Type AR 220 for Preventing Excessive Output from an Amplifier, p. 113. "Super-Responsive Graphers" with or without Automatic Change of Chart Speed.-Everett, Edgeumbe and Company, p. 285. A Photoelectric-Mechanical Harmonic Analyser.-Dietsch and Evideo 52
- Fricke, p. 53. A New Harmonic Analyser [Synchronous Disc and M.C. Voltmeter].
- A New Harmonic Analyser [Synchronous Disc and M.C. Voltmeter]. --Gates, p. 228.
 Harmonic Analysis of Oscillatory Phenomena (Mathematical Processes: Methods of Pichelmayer and Schruttka and of Zipperer]. --Krönert, p. 517.
 Harmonic Analysis: see also Analysis, Integration.
 Supplying Atmospheres of Known Humidity.--Walker, p. 341.
 Hypernik--Its Uses and Limitations.--Wentz, p. 52.
 The Control of Ignition-Coil Discharge Characteristics.--Finch and Sutton p. 982

- The Control of Ignition-Control Discharge Characteristics.—Finds and Sutton, p. 282.
 A New Type of Impedance Unit [Filter Unit from Twisted Pairs of Conductors Encased in Shielding].—Allen, p. 577.
 Prevention of Frequency Variation due to Thermal Expansion and Contraction of Inductance Coils with Varying Loads, by means of a Compensating Current.—Telefunken : Roosenstein, p. 284. Variable Inductors for Bridge Measurements [10:1 Ratio, 0.005

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 The Electrical Strength of Insulating Materials under Mechanical Strain.—Akabira and Gemant, p. 637.
 Insulating Materials—Some Recent Developments [Elephantide Press-Papers, Alkyd Resins, etc.].—Dunton, p. 227.
 A New Industrial Insulating Material: the Lambert Insulating Concrete.—Ferrier, p. 516.
 Losses in Commercial Insulating Materials [and a Comparison between the Maxwell-Wagner and Debye Theories].—Kirch, p. 52.
- p. 52.
- A New Compressed Insulating Material [Synthetic Resin and Linen Aggregate].—Römmler Company, p. 460. A New Insulating Material from Aluminium Oxide.—Siemens & Halske, p. 402.
- A New Insulating Material: Permali [from Wood and Synthetic Resins]—Steinmann, p. 52. An Efficient Insulating Device for Electrostatic Work [Quartz Insulators with Surface Films eliminated by use of Heaters].—
- Telang, p. 340. The Properties of Electrotechnical Insulating Materials and Their Measurement.—Wagner, p. 340. Calan, a New Insulating Material for High-Frequency Engineering,
- Calan, a New **Insulating** Material for High-Frequency Engineering, p. 402. " Calit " and " Calan," Two New Ceramic **Insulating** Materials,
- p. 460.
- A Symposium on Insulating Materials and Their Uses, p. 516. High-Frequency Ceramic [Insulating] Material [giving Accuracy of Dimension, High Dielectric and Mechanical Strengths]. p. 340.
- Insulating Materials : see also Dielectric, Glass and Mica, Glow
- Insulating Materials: see also Directific Orass and mark, vitow Discharge, Insulation, Insulators, Kolonit, Mycalex. Insulating Suspensions or Supports for Short-Wave Components, to avoid Dielectric Losses: the Use of Metallic Windings of High Inductance as Insulators.—Telefunken Company, p. 227. A Summary of Year's Insulation Research.—Whitehead and others,
- p. 227. Capillary Action in Impregnated Paper Insulation.—Whitehead and
- Greenfield, p. 227. Tests on Insulators for Carrier Current Lines.—Boella, p. 52.
- New Pin Insulators for Carrier Current Lines.—Doella, p. 32. New Pin Insulators Free from Radio Interference.—Brown, p. 637. New Liquid Insulator Devised for Transformers [Will Not Mix with Water: Decomposes into Non-Combustible Gases].— Clark: GEC, p. 112. Research brings Remarkable New Liquid Insulator.—"Pyranol."—

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 Critical Remarks on Some New Researches on the Breakdown of Solid Insulators.—Inge, Walther and Wul, p. 516.
 The Molecular Orientation of Liquid and Viscous Insulators and Its Influence on the Anomalous Properties of these Dielectrics at High Frequencics.—Kostomaroff, p. 637.
 On New Integraphs of the Askania Works (Differentio-Integraph, Prism Derivator, etc.].—Picht, p. 173.
 New Instruments for Mechanical Integration, Differentiation, and Harmonic Analysis on the Principle of "Rolled-Up" Abscissae. —Boisseau, p. 517.

- Boisseau, p. 517.
- ---Doisseau, p. 517. The Relaxation Inverter and D.C. Transformer. ---Reich, p. 339. The Parallel Type of Inverter [3-Electrode Hot-Cathode Gas-Filled Tube : including Use for Supplying Power from D.C. Systems to A.C. Radio Sets]. ---Tompkins, p. 402 : see also Converter, Thyratrons.
- Iodide Cells—An Investigation of Cadmium Iodide and Zinc Iodide Types.—Salazar, p. 459. Curves for the Determination of the Permeability of, and Losses
- in, Iron Sheet.—Arkadiew, p. 578. The Magnetic Properties of Electrolytic Iron [in Very Thin Layers].
- -Grigotow, p. 578.

- Magnetisation of Iron by the Superposition of an A.C. Field on a Constant Magnetic Field.—St. Procopiu, p. 515.
 Physical Properties and Structure of the Binary System Iron-Cobalt.—Kusmann, Scharnow and Schulze, p. 52.
 The "Fer-X" [Iron-Cored] H.F. Transformers.—Budich Company, 570.
- p. 579.
- p. 075. Remarks on "Iron Cores for High-Frequency Coils" [Vogt Iron (Ferrocart)].—Nissen: G.W.O.H.: Schneider, p. 515. Calculation of Iron-Cored Coils simultaneously traversed by A.C. and D.C.—Matteini, p. 52. The Approximate Calculation of Iron-Cored Inductances.—Someda: Marcochi a. 515
- Marocchi, p. 515. Iron Cores : see also Cores, Ferrocart, Permalloy, Permeability. Physical Properties of Iron-Nickel Alloys [especially Perminvar].

- Physical Properties of Iron-Nickel Alloys [especially Permeability.
 Dahl, p. 52 : see also Nickel-Iron.
 The Kathetron : a Control Tube with External Grid.—Craig, p. 339.
 Keyboard Telegraph Transmitter and Recorder [for Unskilled Operators].—Painton and Paull, Ltd, p. 285.
 Kolonit, a New Insulating Material from Coal, p. 637.
 A Mechanical Process for the Comparison of Observations by the Method of Least Squares.—Germansky, p. 638.
 The Luminescence of Alkaline Earth Tungstates Containing Lead. —Swindells, p. 458.
 Electro-Plating Copper on Manganin.—Cosens, p. 637.
 A Magnet for Alpha-Ray Spectroscopy with 1 cm Annular Air Gap of Diameter 80 cm, Fields up to 18 000 Gauss].—Cockcroft, p. 340.
- Permanent Magnets.-Elenbaas, p. 460. Contributions to the Design Calculation of Pot Magnets.-Jasse, p. 340. Permanent Oxide Magnet and Its Characteristics .--- Kato and
- Α Takei, p. 579. The Problem of Unipolar Induction and the Electrical Surface
- The Problem of Unipolar Induction and the Electrical Surface Charges on Rotating Magnets.—Slepian, p. 579. New Magnetic Materials for Pupin Coils [Isoperms].—Dahl, Pfaffen-berger and Sprung, p. 637. Isoperme, a Magnetic Material for Telephone Engineering.—Gold-schmidt and Pfaffenberger, p. 281. A New Method for Magnetic Measurements on Strips of Sheet Metal.—Hermann, p. 226. Commercial Materials of Great Magnetic Softness [and a Quick and Accurate Method of Magnetic Softness [and a Quick

- and Accurate Method of Measuring Small Coercive Forces]. Stäblein, p. 112. The Production of Homogeneous Magnetic Fields .- Bühl and

- Coeterier, p. 52. A Magnetic Flux Recorder.—von Auwers, p. 579. The Significance of Internal Tensions in the Theory of Magnetisa-tion Curves.—Preisach, p. 52. Mechanical Models for the Investigation of Electrical Stability

- Problems.—Darious, p. 404. A Method of Cleaning Mercury.—Burstyn, p. 111. Study of the Magnetic Control of the Mercury Arc and of the Static Conversion of Direct into Alternating Current.—Savagnone, p. 110.
- The Theory of Rectification in Hot-Cathode Mercury Vapour Tubes.
- -Brandt and Smith, p. 111. The Mercury Vapour Valve with Polarised Grids, and Its Use as a Reversible Converter.—Ehrensperger, p. 111.
- X-Ray Study of the Density Distribution in a [Mercury Vapour] Discharge Tube.—Ishida and Suetsugu, p. 402. On the Possibility of Binding Mercury Vapour and other Unwanted Vapours in Air by Photochemical Methods.—Klumb, p. 112. The Extinction of Anode-Current Are by Polarised Grid in Mercury Vapour Tubes [Contrary to Usual Belief : New Possibilities].— Kobel 429.
- Kobel, p. 636.
- Rober, p. 606.
 Investigations on Mercury Vapour Discharges.—Lübcke, p. 111.
 Physical Processes in Low-Pressure Mercury Vapour Arcs [Mercury Vapour Rectifiers].—Lübcke, p. 577.
 Magnetic Control of Mercury Vapour Rectifier Tubes [instead of Grid Control].—Reich, p. 339.
 Grid and Plate Currents in a Grid-Controlled Mercury Vapour Tube.—Seletzky and Shevki, p. 329.
 The Importance of Temperature Regulation in the use of Mercury Vapour Factifiers and a Device for this Purpose.—Stanebury.
- Vapour Rectifiers, and a Device for this Purpose.—Stansbury and Brown, p. 459. Notes on the Manufacture of Mercury Vapour Rectifier Tubes.—
- Weiller, p. 459. A Full-Wave Mercury Vapour Rectifier [RCA-83, Cunningham
- CX-83], p. 110.
- Types of Very Small Motors [500 Watts downwards] .- Bunzl-Geemen, p. 281. Sensitive Speed Control for Electric Motors.—Giebe, p. 341. The Development of a Sound-Isolating Base for Motors.—Hull,
- p. 459.
- Mycalex, an Insulating Material for High Voltage and High Fre-quency [with Data] .-- von Nagy, p. 637. quency [with Data].--von Nagy, p. 637. Neon-Lamp Method [Relaxation Oscillation Circuit] for the Measure-
- ment and Registration of Photoelectrically Active and Ionising Radiations.—Stäger, p. 112. A Theory of Neon Tube Operation.—Summers, p. 112.

- A Method for Calculating Transmission Properties of Electrical Networks consisting of a Number of Sections.—Alford, p. 638. On the Structure of the Nickel-Iron Alloys.—Broniewski and Smolinski, p. 515 : see also Iron-Nickel. The Contact Rectifier as Noise-Limiting Device for Telephone Receivers.—Kallmann, p. 638.
- The Suppression of Disturbing Noises by Gaseous Discharge Cut-

- —Schlegelmitch, p. 578. Two New Oscillators for the Radio-Frequency Range.—Grant,
- p. 341
- p. 341. An Oscillograph for Ten Thousand Cycles.—Curtis, p. 225. A Fast and Economical Type of Photographic Oscillograph.—
- The Application of Resonant Shunt Damping to Oscillographs.— Martin and Caris, p. 112. The Two-Element Portable Oscillograph Improved.—Rusher, p. 112. Checking the Performance of Loop Oscillographs by means of the Cathode-Ray Oscillograph.—Lon'ar, p. 634. New Crystal Oven [Heat-Insulated Chamber replaced by Heavy Copper Plate and Small Crystal Heater Ovens : Metallic Expan-sion Varies Carbon Button Microphone Pressure].—Gutterman, p. 52.

- p. 52. Photronic Cell for Temperature Control [of a Crystal Oven], p. 52. What is Anomalous Behaviour of Permeability at High Frequencies ?
- —Arkadiew, p. 226. Calculation of the **Permeability** and Losses in Ferromagnetic Sheets at a Given Frequency [with Formulae and Curves].—Arkadiew, p. 340.
- On the Permeability of Iron at Ultra-Radio Frequencies .- Arkadiew, p. 460.
- Permeability of Iron at Ultra-Radio Frequencies .- Hoag and Jones,
- p. 226. Further Remarks on the Non-Existence of an Anomaly in the Permeability of Iron in the Wavelength Range 84-1 300 Metres, -Wait, p. 637.

- Wait, p. 637.
 Ferro-Inductors and Permeability Tuning.—Polydoroff, p. 393.
 Phanotrons: see Pliotrons (Hull), Rectifier.
 Liaison between the Two General Methods of Preparing Phosphorescent Zinc Sulphide.—Coustal, p. 458.
 Photoelectric Cell: see Amplifying and Recording Small E.M.Fs.
 The Sensitization of Ordinary Photographic Plates to Wave Lengths below 2 500 A : A Simplified Method of Preparing Schumann Plates.—Allen and Franklin: Hopfeld and Appleyard, p. 52.
 The Mechanism of Hypersensitisation.—Carroll and Hubbard, pp. 52 and 984.
- 52 and 284.
- The Effectiveness of Photographic Lavers in Spectrography of All Wavelengths [including Cathode Rays: a Survey].—Eggert, p. 459.
- The Intensification of **Photographic** Records by Subsequent Exposure to Weak Light before Development.—Hartree and
- The Photographic Action of Electrons [and the Effect on the "Threshold" of the Sensitising Process of Oiling the Surface of the Film].—Whiddington and Taylor, p. 52. An Arrangement for Introducing Photographic Plates into a High Vocume and for Removing Them therefore. And resear p. 994.
- Vacuum and for Removing Them therefrom.—Andresen, p. 284. Photography of Faint Transient Light-Spots.—Richardson,
- p. 284. The Most Important Phototechnical Properties of 32 Commercial

- The Most Important Photoechnical Properties of 32 Commercial Types of Film.—Schmieschek, p. 517.
 The Darboux-Koenigs Planigraph.—Nyström, p. 228.
 On the Theory of the Luminous Arc Plasma.—Gábor, p. 111.
 Plastic Materials in Engineering.—Röhrs, p. 227.
 The Crystalline State of Thin Sputtered Films of Platinum.— Thomson, Stuart and Murison, p. 516.
 Study of the Electrical Properties of Thin Films of Platinum obtained by Cathode Sputtering.—Féry, p. 516.
 The Application of the FP-54 Pliotron to Atomic Disintegration Studies.—Harstad, p. 636.
 New Pliotrons, Cathode-Ray Tubes for X-Ray Analysis, Thyratrons and Phanotrons.—Hull, p. 173.

- New Flotrons, Catnode-Ray Tubes for A-Kay Analysis, Tryratrons and Phanotrons.—Hull, p. 173.
 "Banana "Plugs for Laboratory Use.—Bader, p. 113.
 Potentiometers: a Survey.—Brooks, p. 227.
 Distortion of Curve Form by Unsuitable Sliding-Contact Potentio-meters.—Kind, p. 113.
 A New Slide-Wire Potentiometer [Rotatable Cylinder with Contact Poly Robertson 112.
- Ball.—Robertson, p. 113. A Triode Instrument for the Regulation of Electrical Quantities
- according to a Predetermined Programme .- Picker: Fehr, p. 113.

Measurement of Gas Pressure by Negative Glow .- Rentschler,

Measurement of Gas Fressure by Account of Gas Fressure by Account of Gas Fressure by Account of Constraints and the Constraint of Constraints of Constraints and the Constraint of Constraints of Automobile Radio Receivers.— Dunsheath, p. 173.
Logarithmic Protractor.—Yearian, p. 638.
A New Exhaust Pump for High Vacuum [Cenco Aristovac Pump, Molecular Drag Principle].—Cadwell, p. 112.
High-Speed High-Vacuum Diffusion Pumps.—Estermann and Byck, p. 52.

- Figh-Speed High-Vacuum Diffusion **Pumps**.—Estermann and Byck, p. 52. A New Type of Vacuum or Circulating **Pump**.—Harrington, p. 52. Special Apparatus for Continued Operation of High-Vacuum **Pumps** without Superintendence.—Pupp, p. 284. Continuous-Drive Record Paper Holder for Oscillographs.—Fischer,

Continuous-Drive Kecord Paper Fronter for Oschlographs. A Senser, p. 835.
A Pen Recorder for D.C. Millivolts and Microamperes at Energy Levels of 4-5 Microwatts. —Bernade and Lunas, p. 227.
A New Electronic Recorder : New System of Recording using Electronic Means.—Bernade and Lunas, p. 338.
The Field of Application of the "Pege'schreiber" [Automatic Level Recorder] in Telephone Engineering.—Fenyö, p. 638.
A Round Chart Indicating Recorder.—Leeds and Northrup Commany. n. 460.

pany, p. 460. Analyses of Rates of Rotation of Recording Drums.-Blake and

McComb, p. 635. On the Driving Mechanism of Recording Apparatus.--Baltzer,

On the Driving Mechanism of Recording Apparatus.—Baltzer, p. 579.
Rectifier Valve with Cylindrical Anode and Cathode of Tungsten Wire wound round a Calcium Cylinder and continued to a Point near the Anode.—Abadie, p. 110.
The Properties of Copper-Oxide Dry-Plate Rectifiers under Prolonged Test.—Böhm, p. 110.
A Rectifier System for [Plate Voltage Supply of] Broadcast Speech-Input Equipment, using the New -83 [Mercury-Vapour Rectifier].—Bradner Brown, p. 636.
[The Construction of] the Tantalum Rectifier for Battery Charging.—Colebrook, p. 515.
A Phanotron [Hot-Cathode Gas-Filled] Rectifier for Power and Lighting Service.—Currier and Whitney, p. 636.
Current and Potential Relations in Grid-Controlled Rectifiers.— Dailenbach, p. 111.

- Dailenbach, p. 11. Theory of [Mercury Vapour] Arc Rectifiers with Retarded Com-mutation.—Demonstryignier, p. 111. The Selenium Rectifier [Comparison with Copper-Oxide Type].— Fukuda and Saito, p. 515. Selenium or Selenide Rectifier ?—Gripenberg, pp. 53 and 282. The Copper-Cuprous-Oxide Rectifier and Photoelectric Cell.— Groundal n. 515.

The Copper-Cuprous-Oxide Rectifier and Photoelectric Cell.— Grondahl, p. 515.
Copper-Oxide Rectifier used for Radio Detection and Automatic Volume Control.—Grondahl and Place, p. 39.
The Mercury Vapour Valve with Control Grids, and Its Use as a Reversible Rectifier.—Hafner, p. 111.
Fundamental Characteristics and Applications of the Copper-Oxide Rectifier.—Haman and Harty, p. 637.
Thyratron-Controlled Voltage Rectifiers [for Laboratory Use : employing Selsyn Transformer].—Hartman, p. 282.
The Stopping Layer of Rectifiers.—Jusé, p. 636.
The Current Rectifier as an Alternating Current Load.—Klemperer, p. 111.

p. 111.

- p. 111.
 p. 577.
 The Current Rectifier with Capacitative Load.—Klemperer and Strobl, p. 577.
 The Ignitron—a New Controlled Rectifier [Arc started by Spark between Carborundum and Mercury].—Knowles: Westinghouse Company, p. 577. See also below (Slepian).
 Tests on the New Arc-in-Air Rectifier for Very High Voltages and Powers.—Marx, p. 459.
 Measurements on Barrier-Layer Rectifiers [New and Aged : Berg-stein's Classification : Wagner's Theory].—Meyer and Schmidt, p. 295.
- p. 225.
- p. 225. [Experimental] Comparison of the Rectifying Characteristics of Hot-Cathode Mercury-Vapour Rectifier Tubes and High-Vacuum Diodes.—Miura and Utsumi, p. 111. The Current and Voltage Ratios of the Grid-Controlled Rectifiers. —Müller-Lübeck and Uhlmann, p. 459. Investigation of the Copper Oxide Rectifier at High Voltages [Contradiction of the Copper Oxide Rectifier at High Voltages [Contradiction of Cold Emission Theory and Agreement with Joffé-Frenkel Gas Theory].—Nasledow and Nemenow, p. 402. Metal-Clad Mercury Arc Rectifiers in Broadcast Stations.—Sidler, n. 339.

Metal-Clad Mercury Arc Rectiners in Dirautase Statistics—States, p. 339.
A New Method of Starting an Arc [High Resistance "Starter Rods" of Carborundum, etc., for Controlled Rectifiers].—Slepian and Ludwig: Westinghouse, p. 638. See also above (Knowles).
Gas and Vapour Tube Multipliers for Indicator Use [The Use of Grid-Controlled Rectifiers for Amplification of Small D.C. Voltages, as from Thermocouple Pyrometers].—Weiller, p. 459.
Data of Rectifier Valves, Philips, Rectron, Telefunken and Valvo, n. 110.

p. 110. Rectifiers : see also Converters, Crystal, Cuprous Oxide, Inverters, Mercury Arc, Mercury Vapour, Relays, Voltage. Three-Phase Transformer Connections and Their Application to

High-Voltage Rectifying Circuits .- Epperson, p. 459.

The Conductivity of Compressed Mercuric Sulphate [Rectifying Action].—Ścisłowski, p. 577.
The New "K" Tube (Neon Tube particularly designed for Operation of Relays].—Brown, p. 173.
[Tone-Frequency Valve Relay employing] Rectified Reaction.—Harris, p. 113.
An Electron-Tube Time-Delay Relay.—Holloway, p. 640.
Glow-Discharge Relay actuated by Increasing the Electrode Gap.—Landis and Gyr, p. 227.
Gasfiled Relays. Part II.—Practical Applications.—Lewer and Dunham, p. 53.
Non-Linear Circuits [Saturating Reactors in Resonance Circuits] Applied to Relays.—Suits, p. 403.
The Performance of Relays [as regards Variability in Time of Operation].—Tomlinson, p. 578.
Relays for Electronic Devices, p. 235.
Relays for Electronic Devices, p. 235.
Relays for Lectronic Devices, p. 235.

Relay Circuit for Pointer Instruments, replacing Positive Contact by. Spark or Brush Discharge which triggers a Glow Discharge Relay, p. 227.

p. 227. A Commercial ("SSW") Glow-Discharge Relay, p. 113, Relays : see also Glow Discharge. Special Flexible Shaft for Remote Control, p. 579. 100 000-Ohm Wire-Wound Resistances [for Noiseless Operation of Volume Control, etc.].—Clarostat Company, p. 227. Constant High Ohmic Wire Resistances for Heavy Loading.—

Constant High Ohmic Wire Resistances for Heavy Loading.--Jungesblut, p. 284. Variable [Pressure-Regulated] Carbon Resistances.-Le Carbone Company, p. 112. Metallic Electrical Resistance Materials [including Megapyr, Isabellin and Kruppin].--Schulze, p. 637. Controls for 1933 Receivers [particularly Moulded Carbon Variable Resistances and Their Uses].--Wunderlich, p. 460. A New Continuously Variable Resistance, p. 227. A New Resistance Material with Very High Melting Point: the Kanthal Alloys, p. 637. Resistance : see also Manganin. "Monette" High-Resistance Cord, p. 284. The Measurement of the Phase Angles of Shielded Resistors.-Ber-berich, p. 227.

The Measurement of the Phase Angles of Shielded Resistors.—Ber-berich, p. 227. A Resistor for High-Voltage Measurements [made from Thin-Film Carbon Resistances].—Bowdler, p. 637. The Constant Paramagnetism of Metallic Rhenium.—Perakis and Capatos, p. 281. Rhenium, Its Properties and Application, p. 281. An Improved Rheostat [with Screw-Drive Mechanism].—Whitson, n. 113.

p. 113.

Anomalous Dispersion of the Dielectric Constant of Rochelle Salt .-Busch, p. 637.

Busch, p. 637. Measurements of the Dielectric Constant of Rochelle Salt by a New Method.—Oplatka, p. 403. Investigation of the Dielectric. Properties of Rochelle Salt by means of X-Rays.—Staub, p. 403. Conducting Properties of Rubber Strongly impregnated with Lamp Black [and Their Variation with Tension and Compression: Applications to Radio Technique].—Granier, p. 402. A Novel Optical Screen for Classroom Demonstrations [White Cotton Threads stretched Vertically like Harp Strings].—Howey, p. 985.

p. 285.

Screening of a Core-less Oil-cooled Choking Coil by means of an Auxiliary Winding. Part 1.—Hak, p. 226. The Screening of the Magnetic Field of Cylindrical Coils.—Hillers,

Authrary winning. The Terlaid of Cylindrical Coils.—Hillers, p. 281. New Design of High-Wattage Incandscent Lamps made possible by the Development of a Simple and Reliable Method for making a Copper-to-Glass Seal].—Wright, p. 285. The Conductivity of Electronic Semi-Conductors in a Magnetic Field.—Bronstein, p. 402. The Discontinuities of Potential at the Contact of a Semi-Conductor and a Metallic Electrode.—Déchène, p. 515. Electrical and Optical Behaviour of Semi-Conductors. IX. Mechanism and Origin of Conductivity in the Dark and Photo-electric Conductivity of Cuprous Oxide.—Engelhard, p. 636. Report on the Theory of Semi-Conductors.—Fowler, p. 515. Electromagnetic Shielding at Radio Frequencies.—King, p. 206. Experiments on Electromagnetic Shielding at Frequencies between One and Thirty Klicoycles.—Lyons : King, p. 403. An Instrument for Testing Windings for Short-Circuited Turns.— Geyger, p. 113. A Shorted-Turn Indicator [e.g. for Testing Voice Coils of M.C. Loud Speakers].—Seright, p. 517. A Signal Generator for the New Receiver Tests.—Thiessen, p. 341. Magnetic Skin Effect in Laminated Iron with an Air Gap.—Kaden,

Magnetic Skin Effect in Laminated Iron with an Air Gap .- Kaden, p. 226.

The Theory of the Skin Effect.—Rothe, p. 498. Skin Effect in a Stratified Cylinder of Circular Section.—Strutt, p. 269.

Skin Effect with Direct Current.—Weber, p. 516. A New Substitute for the Slide Rule.—Ravigneaux, p. 228. A Study of the Probable Error of Slide Rules.—MacAdam, p. 53.

- Sodium-Filled Tubes as Electrical Conductors for Large Currents .---
- Sodium-Filled Tubes as Electrical Conductors for Large Currents.— Dow, p. 284.
 Spiral Springs [New Theory, New Methods of Attachment, etc.].— van den Broek, p. 53.
 The Stabilisation of Potentials of the Order of 1 000 Volts by means of Positive Corona Discharges : a Portable Apparatus for Use with Ion Tube Counters, etc. [using a Spark Coil as Supply Source].—G. Medicus, p. 638.
 On the Quantitative Theory of the Wimshurst Static Machine : of the Toepler-Holtz Static Machine.—Simon, p. 285.
 Progressive Lightning : a New Stereoscopic.—Boys, p. 389.
 Composition of Grids for Positive Plates of Storage Batteries as a Factor influencing the Sulphation of Negative Plates [and the Effect of the Presence of Antimony].—Vinal, Craig and Snyder, p. 579.

- p. 579.
- p. 5/3. Focusing Stroboscopic Measurements by means of Short Voltage Impulses [as the Source of Lamp Illumination].—Fucks and Weyrauch, p. 113. A Tuning-Fork-Controlled Stroboscopic Light Source.—Kluge,
- p. 113. The Mercury Arc as an Actinic Stroboscopic Light Source.—Edgerton
- and Germeshausen, p. 113. A New Material for Various Radio Purposes.—" Svea " Iron.— Todd, p. 113.
- Todd, p. 113. Special Iron for Vacuum-Tube Electrodes ["Svea Metal "], p. 281. Synchronisation of Motors: the Prevention of Hunting [using an Elastically-Connected Flywheel, a Photoelectric Cell and Thyra-trons].—Lichine: Béghin, p. 578. Synchronoscope: see Cathode-Ray. The Nevson Tangraph Rule, p. 460. Outline of a Theory of the Technique of Temperature Regulation.— Lang. n. 349.

- Outline of a Theory of the Technique of Temperature Regulation.— Lang, p. 342.
 On the Temperature Coefficient of the Electrical Resistance of Silicon, and a Thermoelectric Phenomenon of Unipolar Sub-stances.—Bedel, p. 112.
 The Construction of Thermoelectric Piles.—Cotton : Égal, p. 341.
 New Way of Making Use of Thermoelectric Phenomena [Many Thermoeluctions in Series].—Egal, p. 227.
 An Iridium-Rhodium Thermoelement for Temperatures up to 2 000°C.—Feussner, p. 342.
 A Precision Aperiodic Thermostat [to avoid Rapid Local Tempera-ture Fluctuations often undetected by Thermoenter].—Schmitt, n. 52.

- p. 52. Modifications in the Haughton-Hanson [Hot and Cold Bulb] Thermostat, p. 52.
- Thermostat, p. 52. An Automatic Regulating Device for Thermostats or Adiabatic Calorimeters.—Rieche: Semm, p. 112. Calculations on Thyratrons [on Basis of Richardson Equation: Desirable Relations Found].—Frenkel, p. 459. Characteristics and Functions of Thyratrons.—Hull, p. 339. The Temporal Course of the Ignition of Ionic Valves [Thyratrons].—

- The Temporal Course of the Ignition to Toric Variation (1997). Klemperer, p. 459. The Single-Tube Thyratron Inverter [and Its Applications, par-ticularly as Generator of Saw-Tooth Voltage for Linear Time Base or Spot-Welding Control].—Livingston and Lord, p. 459. A Life-Test Power Supply Utilising Thyratron Rectifiers.—Lord,
- p. 577.
- Harmonic Commutation for Thyratron Inverters and Rectifiers.-Harmonic Commutation for Fugueton interest of the set o

- Reich, p. 53.
- Thyratrons: see also Arcs, Converters, Gas-Filled, Inverters, Pilotrons, Rectifiers. Electronic Timer for Very Short Intervals [Double Thyratron Circuit suitable for use with Photoelectric Cell].—Lord, p. 113. An Automatic [Photoelectric] Time-Recorder.—Richards and Wood p. 52
- An Automatic [Photoelectric] Time-Recorder.--Kicnards and Wood, p. 53. A Time Transformer for the Automatic Registration of Short Times.
- A time transformer for the Automatic Registration of Short Times. —Steenbeck and Strigel, p. 225.
 Tuned-Transformer Coupling Circuits [Low-Loss Air-Core Transformers, as used in I.F. Amplifier of Field Strength Measuring Set].—Christopher, p. 341.
 Light-Weight Transformers for Aircraft [for Transmitters and Re-ceivers].—Grant, p. 226.
 A Current Transformer for Low Radio Frequencies [for Use in the Measurement of Low Redio Frequencies]
- Measurement of Currents of 10-500 A at 60 kc/s, in Conductors at Potentials 10 000 v above Earth].—Hilton, p. 638. Transformers with Peaked Waves [e.g. for Neon Lamp Strobo-scopes].—Kiltie, p. 226. The Design of an "Error-Free" Current Transformer [Constant
- Permeability by use of Two Magnetic Circuits working respectively on the Concave and Convex Parts of Their Magnetisation Curves Schwager, p. 515.

- Power Transformer Testing.—Shea, p. 173. [Air-Cored] Transformers with Variable Coupling.—Siegel, p. 443. VDE Rules for Design and Testing of Small and Low-Voltage Transformers.—Verband Deutscher Elektrotechniker, p. 460. VDE Rules for Design and Testing of Small and Low-Voltage Transformers, p. 340.

- Current Transformer of Toroidal Type, giving Limited Secondary Current even with Excessive Primary Current, p. 340. Contribution to the Calculation of the Optimum Dimensions of
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 A Mercury Sealed Gas Valve.—Exist, p. 225.
 On the Regulation of Voltage [Various Systems, including the Tirrill Regulator].—de Querquis, p. 112.
 The Use of Triode Vacuum Tube Rectifiers to Supply Constant Voltage.—Richards, p. 636.
 Triode Regulators [for Rapid and Accurate Voltage Control : Philips Company].—Voorhoeve and de Jong, p. 112.
 Diode Regulators—a Simple Method of Voltage Control, p. 341.
 Automatic Voltage Regulation by a Recording Voltmeter with Predetermined Limits inscribed in a Conductive Ink.—Fehr, p. 638. p. 638.
- Methods of Power-Supply Voltage Regulation during Keying, p. 112.
- Voltage Stabilisation : the Mechanism of Voltage Regulation by means of Gas Discharge Tubes.—Colebrook, p. 577. A Simple Method of Observing High-Frequency Voltage Wave Forms [Cathode-Ray Oscillograph and Rotating Mirror].—Bab, p. 224.

- p. 2625.
 Wave-Forms: see also Cathode-Ray.
 Discussion of the Action of a Wehnelt Cylinder using Potential Theory. --Wendt, p. 635.
 Heat-Resistant Insulated Wire [Vega Chrom-oxide Wire], p. 341.
 The A.C. Resistance of Straight Wires of Circular Section composed of Several Concentric Layers [e.g., Tinned or Oxidised Copper Oxide Device Device

- of Several Concentric Layers [e.g., Tinned or Oxidised Copper Wire].—Ekelöf, pp. 323-324. Tests on Stranded Wires.—List, p. 284. Secondary Electrons in X-Ray Tubes [Avoidance of Their Effects].— Bouwers and van der Tuuk, p. 112. X-Ray Tube Input Control.—Harper, p. 225. A Metal X-Ray Tube [using Stainless Steel, Pyrex Glass, Sealing Wax. Absence of Ground Cone Joints and the Use of Vacuum Grease].—Ksanda, p. 112. Operation of Thick-Walled X-Ray Tubes on Rectified Potentials [Blocking Action of High Negative Charge on Cold Glass Walls]. —Taylor and Stoneburger. p. 284.
- Taylor and Stoneburner, p. 284.

STATIONS, DESIGN AND OPERATION

Ultra-Short-Wave Developments in Aircraft : a Description of Equipment for Duplex Telephony on One Aerial.-Gee, p. 404.

Aircraft Radio [Survey].—Okada, p. 639. Projected Ultra-Short-Wave ["Microwave"] Service for Aircraft

- Alteratt Ratio [Survey].—Okada, p. 606.
 Projected Ultra-Short-Wave ["Microwave"] Service for Aircraft Information between England and France, p. 286.
 The Clear Channel in American Broadcasting [Is it Still Essential ?].
 —Broadcast Committee, I.R.E., p. 342.
 Announcers and Announcing.—Lebede, p. 229.
 The Prospects of Long-Wave Broadcasting in South-Eastern Australia.—Munro and Green, p. 579.
 Radio Communication in Aviation [a Survey].—Brenot, p. 460.
 Adaptation of the Baudot Apparatus to Long- and Short-Wave Radiotelegraphy.—Verdan, p. 639.
 Bisamberg : see Vienna.
 The Boat Race : Description of the Apparatus used on the B.B.C. Launch, p. 342.
 The Fading-Diminishing ["One-Wire"] Aerial of the Breslau Broadcasting Station.—Eppen and Gothe, p. 394.
 The Breslau High-Power Broadcasting Station [and the "One-Wire" Aerial Results], p. 114.
 Development of Broadcast Transmissions [International Organisa-tion, Administration, etc.].—Braillard, p. 404. See also under "Miscellaneous." tion, Administra " Miscellaneous.

- Miscellaneous."
 Long versus Short Broadcast Waves.—Byrne, p. 229.
 The Required Minimum Frequency Separation between Carrier Waves of Broadcast Stations.—Eckersley, p. 285.
 Proper Sites for Broadcast Stations : a Radical Proposal to Improve Receiving Conditions [Transference of Stations to Sites near Centre of Territory Served].—Horn, p. 342.
 Some New Foreign Broadcasting Stations [Proadcasting] Radio Stations.—Eppen, p. 342.
 Ten Years of Broadcasting.—Fleury, p. 342.
 How should the Sound Archives of Broadcasting be Used ?—Lebede, p. 229.

- p. 229.

- The Technique of Broadcasting.—Part I., p. 114. China's First High-Power Broadcasting Station, at Nanking, p. 114. The Coltano Radio-Maritime Centre.—Pession, Montefinale and Marzoli, p. 114. New Milestones in Commercial Wireless.—Chetwode Crawley,
- p. 174. Some Experiments on Common-Frequency Broadcasting.—Takata and Kinase, p. 53.

Stations, Design and Operation.

- Time Delay Effects in Synchronous [Common-Wave] Broadcasting. Aiken, p. 460.
- The Question of the Choice of **Common-Wave** Systems [Synchron-ised or Unsynchronised].—Gerth, p. 391.
- Runge, p. 285. Common-Wavelength Relay Broadcasting [Nature and Possibilities].
- -Wells, p. 404. Supervisory and Control Equipment for Audio-Frequency Ampli-fiers.-Sohon, p. 286. Experimental Results on a Radio Broadcasting System using
- Distribution Networks of Electric Supply.—Miura, p. 639, Short-Wave Broadcasting in the Dutch East Indies.—Kuyck,
- p. 497. The Radiation Diagram of the Eiffel Tower Wireless Station. David, p. 173. Six Months of Empire Broadcasting.—Ashbridge, p. 460.

- Empire Broadcasting —Smith Rose, p. 174. The Empire Transmitting Station : Technical Details of the New Short-Wave Equipment, p. 114. Christmas Greetings Over the Empire : How the Broadcast was
- Constraints Greetings Over the Empire : How the Broadcast was Done, p. 174. Empire Broadcasting—Details of Equipment at Daventry—New Short-Wave Transmitters, p. 114. The Empire Broadcasting Station, p. 174. System for the Elimination of Effects of Fading and Atmospheries in Wirk Second Telegraphy, wing Simal Reputition Method.
- in High-Speed Telegraphy, using Signal Repetition Method.— Telefunken: Schröter, p. 230. Transoceanic Short-Wave Services: the Prediction of Day-to-Day
- Transuctant Short-wave Services : the Frequency and the Magnetic Activity.— Brown : National Broadcasting Company, p. 639.
 A Frequency Monitoring Unit for Broadcast Stations.—Coram, p. 174 and 342.
 The German Stations for Oversea Service.—Habn, p. 230.
 The Completion of the German Periodection Magnetic.

- Jipp, p. 286. The International Organisation of Radio Communications: Organ-iations, Conventions and International Regulations.—Adam,
- p. 460. The Development of Broadcasting in Italy, p. 638

- The Development of Broadcasting in Italy, p. 638. Land-Line Circuits for Broadcasting : Equilisation of Land-Line Circuits, p. 579. The League of Nations Wireless Station.—van Dissel, p. 638. The Marconi Short-Wave Telephone-Telegraph Installation of the League of Nations.—Marconi Company, p. 286. The Lucerne Wave Allocation Plan.—Giess, p. 518. The European Radiocommunications Conference at Lucerne, 1933. —Reyval, p. 639. Lucerne Wave Plan : Some Continental Opinions, p. 518.

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- The Madrid Conference and the Regulation of Radio Communication

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- p. 270. Micro: see also Aircraft, Sardinia, Ultra-Short. Note on an Impulse Indicator (for Monitoring Modulation of Wireless Transmitters and Sound Films].—Rocard, p. 639. "France-Algeria" Multiplex and Secret Radiotelephone Service.—
- Borias, p. 638. Music Transmission over Short-Wave Commercial Radio-Telephone
- Circuits.-Gracie, p. 404. A Broadcasting Service for Portugal : Establishment of a State
- Monopoly, p. 518.

- Field-Strength Charts of Poste-Parisien and Radio-Paris .- David, p. 461. The Working of Radioelectric Services [Survey of Ten Years].

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- p. 229. Speech from Ship to Shore.—Bennington, p. 114. Short-Wave Transmission to South America (Survey of Transmis-sion Conditions, etc.).—Burrows and Howard, p. 229. Experimental Contribution to the Study of the Propagation of Short Waves (Dased on Paris-Buenos Ayres and Paris-New York Services).—Maire, p. 404. Particulars of the Principal Short-Wave Stations of the World.— Namba n 124.
- Namba, p. 174. Method of Calculation of Field Strengths in High-Frequency [Short-Wave] Radio Transmission.—Namba and Tsukada, A p. 560.
- Long-Distance Short-Wave Services [a Survey of Ten Years] .-Villem, p. 342. Transoceanic Reception of High-Frequency Telephone Signals
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 Short Wave : see also Dutch E. Indies, Sardinia.
 Simultaneous Broadcasting [Land-Line Technique].—Lyall, p. 638.
 Simultaneous Telegraphy and Telephony on Short-Wave Circuits.— Thierbach, p. 114.
 Simultaneous Telephony and Telegraphy on Short Waves.—Lüschen, n. 114.

- p. 114.
- p. 114.
 The Use of a Control Frequency outside the Speech Band for Controlling Receiver Amplification and simultaneously for Telegraphic Communication —Telefunken: Runge, p. 342.
 The Tatsfield Checking Station: Development of the B.B.C. Listening Post, p. 342.
 A Telephone System for Harbour Craft: Fishing Industry Adopts Marine Telephony.—St. Clair: Woodworth, p. 54.
 Radio-Telephony [Survey for 1932, including the "Compandor" Device].—Falkner, p. 330.
 Mobile Radiotelephony [Passenger Ships, Whaling Ships, frawlers, Aircraft, Trains].—Loring and Buttner, p. 114.
 The Use of Telephonic Groutis for Special Transmissions: Broadcast Relaying: Picture Transmission: Conferences by Telephone.—Höpfner, p. 229.
 The "Radio Trains" of the National Society of Belgian Railways.—Katel, p. 639.

- The "Radio Trans" of the National Society of Beigian Rauways. --Katel, p. 639. High Power Trarsmission and Reception at One Station [Beam Station at Salisbury, Rhodesia].--Marconi Company, p. 230. Experiments on Ultra-High-Frequency Communications [on 8.2-Metre Wave from Summit of Mt. Fuji].--Nakai, Kimura and Unra 1720

- Ueno, p. 173. Some Practical Experiments on Ultra-Short Waves [7.75 Metres : B.B.C. and Marconi Company's Preliminary Tests].—Ashbridge, p. 229.
- Ultra-Short Waves and Their Use in Radio Communication .-Carrara, p. 114. The Ultra-Short-Wave Service between Corsica and the Continent.—

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 Ultra-Short Radio Waves and the Cardiff-Weston-super-Mare Radio Link.—Nancarrow, p. 228.
 Broadcasting on [Ultra-Short Waves of] 7.85 Metres : Experi-mental Work in Amsterdam.—Nordlohne : Philip's Company, pp. 229, 342, and 404.
 Five Metre [Ultra-Short-Wave] Work for Amateurs.—O'Hef-ferman and Morgan, p. 461.
 The Radio-telephone Service by Ultra-Short Waves between the Continent and Corsica.—Picault, p. 54. Also de C., above.
 One More Step in Universal Communication [the "Transceiver," a Two-way Transmitter and Receiver weighing 22 Pounds with Battery Unit, for Ultra-Short Wave around 5 Metres].—RCA Victor, p. 173. Victor, p. 173.
- Communication Tests on Ultra-Short Waves between Small Islands and Main Land.—Uda, Obata, Arisaka and Seki, p. 173. Tests for Broadcasting and for Some Other Special Communication

- by Ultra-Short Waves.—Uda and Arisaka, p. 173. The Ultra-Short-Waves.—Uda and Arisaka, p. 173. "Ultra-Short-Wave Link across the Bristol Channel, p. 114. "Ultra-Shorts " from the Air.—Morgan, p. 517. Ultra-Short and Ultra-High : see also Aircraft, Micro. The Vienna [Bisamberg] High-Power Broadcasting Station.— Mover a 638 Meyer, p. 638.
- The New Vienna Broadcasting Station.—Telefunken, p. 286. The Bisamberg (Vienna) High-Power Broadcasting Station with Reflector Tower.—Telefunken, p. 229.

Stations, Design and Operation.

Note on the Field Intensity of the Marconi Broadcasting Station erected at Warsaw [Comparison of Observed Results with the Eckersley "Modified Watson Diffraction Formula "].—Eckersley,

p. 113. Wireless Equipment in British Warships.--Garner, p. 404 West Regional Broadcasting Station in Great Britain, p. 404.

GENERAL PHYSICAL ARTICLES

The Laws of Action at a Distance in Electricity.—Abraham, p. 639. The Equilibrium of Atoms and Ions Adsorbed on a Metal Surface.

In e Equilibrium of Atoms and ions Adsorbed on a Metal Surface. —Evans, p. 343.
 Phase Boundary Potentials of Adsorbed Films on Metals.—Whalley and Rideal : Jacobs and Whalley, p. 579.
 On the Cold Cathode Vacuum Arc.—Newman, p. 55.
 Arc, Spark and Glow : A Note on Nomenclature.—Thomson, p. 55.

On Atoms of Action, Electricity and Light.—Fleming, p. 54. Electrical Barkhausen Effect in Crystals of Rochelle Salt.—Kluge

and Schönfeld, p. 287. On the Relation between the Integral and the Differential Biot-Savart Law.—Greinacher, p. 114. Recombination Radiation in the Cassium Positive Column.—Mohler,

p. 580. The Adsorption of Caesium Atoms on Tungsten. —Langmuir, p. 343. The Nature of Adsorbed Films of Caesium on Tungsten. Part I. The Space Charge Sheath and the Image Force.—Langmuir, p. 343.

Accommodation Coefficient of Gaseous Ions at Cathodes .- Compton.

- Accommodation Commenter of Accommodation Coefficient p. 115. Interpretation of Phenomena due to Accommodation Coefficient of lons at Cathode Surfaces.—Compton, p. 343. On the Mobility of Electrical Charge Carriers under the Simultaneous Influence of Strong Electric and Magnetic Fields.—Kugler, Ollendorff and Roggendorf, p. 461.
- Novement of Charged Particles in a Field of Suddenly Changing Potential.—Persico, p. 461. Physics and the Method of Coincidences.—Bender, p. 54. Demonstration of the Existence of the Multiple Compton Effect.—

Demonstration of the Existence of the Multiple Compton Effect.— Hulubei, p. 287.
Theory of the Conductivity of Polarisable Media:—Jaffé, p. 287.
The Electronic Conductivity of the Copper Oxides.—Le Blanc, Sachse and Schöpel, p. 579.
Problems of Electrical Images in Dielectrics. I.—Weigle, p. 54.
Dielectric Constant and Particle Size.—Williams and Oncley, p. 230.
On some Applications of the Absolute Differential Calculus to Physics.—Kaplan, p. 230.
On an Analexy between the Direc Electron and the Electromagnetic

- Charles and the second s
- b. Dirac's New Theory of the Electromagnetic Field.—Schubin, p. 518.
 The Influence of Circuit Constants and Frequency on Characteristics of Gas Discharges at Low Pressures (Part VI).—Asami, p. 580.
 The Explanation of Luminous Phenomena in Spark Discharge

In Explanation of Luminous Phenomena in Spark Discharge through Gases.—Prucks, p. 230. Gas Discharge and Breakdown.—Rogowski, p. 115. Corona and Spark Discharge in Gases.—Stephenson, p. 579. High-Frequency Electric Discharge in Gases.—Wilson, p. 461. Electrodeless Discharges in Uniform Fields.—Yarnold, p. 343. Energy turned into Mass for First Time in History : Atom Dis-integration Experiments confirm Einstein's Theory of Mass-Energy turned into data and the state of the state of the state of the state Energy turned into the state of the st

Energy Equivalence.—Bainbridge, p. 405. Experiments to Determine the Total Intensity of the Earth's Magnetic Field from the Time of Rotation of Slow Electrons.— Stehberger, p. 518. The Value of *elm*.—Birge, p. 343. Determination of *elm* for an Electron by a New Deflection Method. —Dupmington p. 342.

Determination of e/m for an Electron by a New Deflection Method. --Dunnington, p. 343. A Determination of e/m by means of Photoelectrons excited by X-Rays.--Kretschmar, p. 343. The Most Probable Values of the Atomic Constants e and h.-Ladenburg, p. 343. The Most Probable Values of e, e/m and h.-Shiba, p. 343. On Mosermonator of h/m for Theorem 4 like Distance B. Schutz

On Measurements of e/m for Thread-like Electron Beams .- Siebertz, p. 115.

Theory of Electric Charge.—Eddington, p. 54. The Kinetics of Electrode Processes. Part II.—Reversible Re-duction and Oxidation Processes.—Butler and Armstrong, p. 287.

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The Electromagnetic Field of a Moving Uniformly and Rigidly Electrified Sphere and Its Radiationless Orbits.—Schott, p. 342. Scattering of Electrons by Ions and the Mobility of Electrons in a Caesium Discharge.—Boeckner and Mohler, p. 405.

The Foundations of Geometrical Electron Optics.—Brüche, p. 230. Electron Beam and Gas Discharge.—Brüche, pp. 283-284. Extension of Woo's Formula. Intensity of the Light diffused by an Electron in Motion.—Cannata, p. 405. Remarks on the Magnetic Moment and the Moment of Rotation of the Electron.—de Broglie, p. 54. The Linear Momenta of Electrons in Atoms and in Solid.Bodies, as Revealed by X-Ray Scattering.—Du Mond, p. 405. Electrical Charges Smaller than That of the Electron.—Ehrenhaft, p. 287.

p. 287. The Possible Existence of a Charge smaller than that of the Electron.

 The Possible Existence of a Charge smaller than that of the Electron. —Wasser : Ehrenhaft, p. 639.
 Remark on the Space-Charge Field of the Gas-Concentrated Electron Beam.—Engel, p. 115.
 On the Conservation of the Quantity of Motion in the Processes of Electron Collision.—Goldstein, p. 115.
 Emission of Electrons from Metals under the Action of Mono- chromatic X-Radiation.—Hase, p. 343.
 On the Velocity Distribution of Secondary Electrons from In- sulators.—Kalckhoff, p. 343.
 Secondary Electron Emission from Tantalum [on Bombardment by Lithium Ions].—Utterback and Williams, p. 343.
 Electron Diffusion, Electron Attachment, and the Ageing of Negative Ions in Commercial Nitrogen at Atmospheric Pressure. —Zeleny, p. 55. -Zeleny, p. 55. Electron : see also Dirac. Electron Theory of Metals [Mathematical Paper on Present State : including Thermionic and "Cold" Emission].—Peierls, p. 461. Notes on Some Electronic Properties of Conductors and Insulators. —Fourier p. 570

-Fowler, p. 579. On the [Quantum Mechanics] Theory of Electronic Semi-Conductors.

 Bronstein, p. 461.
 An Elementary Theory of Electronic Semi-Conductors, and Some of Their Possible Properties.—Fowler, p. 579.
 The Passage of Photonic Rays through Atoms [and the Ether as a Corpuscular Structure whose Corpuscles are Atoms of Zero Atoms [and the Ether as a Corpuscular Structure whose Corpuscles are Atoms of Zero Atoms [and the Structure whose Corpuscles are Atoms of Zero Atoms [and the Structure] Atomic Number with Nuclei formed of a Proton and an Electron]. —Posejpal, p. 55. The Polarisation of the Fluorescent Light of Pure Mercury Vapour

[and the Depolarising Effect of a Magnetic Field].-Kastler, p. 639.

p. 639.
 The Fundamental Particles.—Langer, p. 54.
 Contemporary Advances in Physics: High-Frequency Phenomena in Gases.—Darrow, pp. 174 and 230.
 Gravitation and Electricity.—Viney and Leybourne: Willis, p. 343.
 The Twenty-Third Kelvin Lecture: "The Work of Osiver Heavi-side."—Sumpner, p. 174.
 The Hydrodynamic Theory of Electro-Magnetism.—Prunier, p. 54.
 The Principle of Indefinitences.—Darrow, p. 158.

side: —Sumplet, p. 173.
The Hydrodynamic Theory of Electro-Magnetism.—Prunier, p. 54.
The Principle of Indefiniteness.—Darrow, p. 518.
Course of Current and Voltage in Insulating Materials with One or Several Movable Thin Layers of Charge.—Schumann, p. 461.
Measurement of the Townsend Coefficients for Ionisation by Collision.—Sanders, p. 580.
Ionisation by Positive Ions.—Townsend and Jones, p. 343.
Electrical Conductivity of Ionised Gas in the Presence of a Magnetic Field.—Cowling, p. 461.
Investigations of the "Electrical Diffusion" of the Ions in Gases with Unipolar Charge.—Woloklewitsch, p. 287.
The Definition of a Magnetic Field on the Absorption Rays of Iodine [and Its Destructive Action on Fluorescence].—Agarbiceanu, p. 287.
On the Influence of a Transverse Magnetic Field upon the Resistance

On the Influence of a Transverse Magnetic Field upon the Resistance of Liquid Metals.—Fakidow and Kikoin, p. 579. Atomic Magnetism.—Chevallier : Cabrera, p. 287. A Common Misapprehension of the Theory of Induced Magnetism.

A common Misapprenension of the Theory of Induced magnetism, —Wilberforce, p. 287. Generalisations of Maxwell's Theory.—Viney, p. 54. Michelson Interferometer Experiment : Miller's Result on Mount Wilson explained as the Esclangon Effect.—Carvallo, p. 174. The Chemical Nature of the Neutron.—Achalme, p. 287. The Neutron.—Kurie, p. 405. Artificial Production of Neutrons.—Lauritsen, Crane and Soltan, p. 927

Artinetal Production of Neutrons.—Lauritsen, Craite and Soltan, p. 287.
 The Mass of the Neutron [consisting of One Proton and One Electron of Negative Energy].—Placinteanu, p. 518.
 Theoretical Considerations on the Constitution of Neutrons, Positive Electrons and Photons : the Existence of Negative Protons.— Desitive run at 2000

Placinteanu, p. 639. Synthesis of the Works of Newton, Fresnel and Maxwell.—Sevin, p. 639.

Non-Canonical Transformations and the Electromagnetic Field.— Rumer, p. 518. Non-Conducting Modifications of Metals.—Kramer and Zahn,

p. 115. The Problems of Perturbations and Self-Consistent Fields.—Brillouin,

p. 54.

An Effect of Space-Charge in Probe Analysis of a Plasma.-Sloane and Emeleus, p. 639.

General Physical Articles.

The Formation of the Maxwell Distribution in a Langmuir Plasma. -Gábor, p. 230. Electrostatic Theory of a [Langmuir] Plasma.-Gábor, p. 639.

- Langmuir's Plasma.—Seeliger, p. 55. Paramagnetic Rotatory Polarisation [especially the Enormous Rotating Power of Tysonite].—Becquerel and de Haas, p. 115. Positive and Negative Electrons Apparently Produced in Paris [Support to Millikan's Photon Theory of Cosmic Rays].—Langer :
- Anderson, p. 461. The Positive Electron.
- The Positive Electron.—Anderson, p. 405. Some Photographs of the Tracks of Penetrating Radiation [showing Positive Electrons].—Blackett and Occhialini, p. 343. New Evidence for the Positive Electron.—Chadwick, Blackett and
- Occhialini, p. 405. Contribution to the Study of the Positive Electrons.—Curie and
- Joliot, p. 405. The Origin of the Positive Electrons.—Curie and Joliot, p. 518.

- The Origin of the Positive Electrons.—Curie and Joliot, p. 518. Positron formally Introduced; Negative Proton Predicted.— Anderson, p. 405. Free Positive Electrons ["Positron" suggested as Name: Lose energy more rapidly than "Negatrons" in passing through Matter].—Davis: Anderson, p. 405. Positive Electrons and the Existence of Protons [Dirac's Theory of the Holes: the Proton as a "Hole with a Neutron"].—Mandel, p. 518 p. 518.
- Electrostatic Deviation and Specific Charge of the Positive Electron.
- --Thibaud, p. 579. Some Evidence indicating a Removal of Positive Ions from Cold Surfaces by Electric Fields.--Beams, p. 115. Emission of Positive Ions from Cold Surfaces under the Influence
- of Strong Electric Fields.—Harper, p. 115. A New Expression for **Poynting's Radiation Vector**.—Prunier, p. 639.
- Probability and the Exponential Laws of Physics [Derivation from Probability and the Exponential Laws of Physics [Derivation from Poisson's Probability Equation].—Holmes, p. 518. The Complexity of the Proton and the Mass of the Neutron [Proton composed of Neutron and Positive Electron].—Curie and Joliot,
- p. 579.
- Quantum Theory of Dispersion (Continued). Parts VI and VII.-Breit, p. 579.
- Quantum Electrodynamics .- Dirac, Fock and Podolsky, On p. 518. The Lagrangian in Quantum Mechanics.—Dirac, p. 342.
- A Further Point of Analogy between the Equations of the Quantum Theory and Maxwell's Equations.—Fahmy, p. 287. On the Quantum Theory of the Diffusion of Electrons.—Goldstein,
- p. 114 Quantum Theory of Inelastic Collisions of Electrons .--Goldstein,
- p. 579.
- p. 579.
 The Quantum Theory of Semi-Conductors [a Survey].—Hill,
 p. 461.
 On the Function of Quantum Mechanics which corresponds to a Given Function in Classical Mechanics.—McCoy, p. 114.
 Quantum Mechanics of Collision Processes.—Morse, p. 55.
 Experimental Establishment of the Relativity of Time.—Kennedy
- and Thorndike, p. 174. Ritz's Electrodynamic Theory.-
- -Hovgaard, n. 579.
- Observation with the Eye of a Schrot Effect for Photons.-Barnes and
- Czerny, p. 461.
 Semi-Conductors: see also Electronic, Quantum.
 The Field Distortion of a Plane Spark Gap, crossed at Constant Voltage by an Ionising Electron Layer.—Sämmer, p. 461.
 On the Flow of Electric Current in Semi-Infinite Stratified Media.— King, p. 286.
 Superconductivity of Tin at Radio Frequencies.—Sibbee Scott

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p. 286. The Wave-Mechanical Theory of the Harmonic Oscillator.—Oseen,

- p. 286. The Analysis of Compound Wave Forms.—Thompson, p. 230. On the Electromagnetic Field of the Wave of Light.—de Broglie, p. 114.

MISCELLANEOUS

- On Abstracts Journals.—Pegram, p. 640 : see also Physical Society. Scientific Instruments and Aeronautics.—Wimperis, p. 282. Yearly Report of the Electrical Engineering and Wireless Division of the German Aircraft Research Establishment.—Fassbender,

- of the German Anteian Account account of the German Anteian Account of Solving Algebraical Equations.—Lahaye, p. 287. Amplifilter : see Carrier. An Amplifying Lever for the Measurement of Small Displacements An Amplifying Lever for the Measurement of Small Displacements [such as the Deformations of Piezoelectric Plates] .- Fink and Fox, p. 463.
- Physico-Chemical Method of Analysis in an Organic Solution 1 Measuring the Dielectric Constant.—Chrétien and Laurent, p. 117. The Differential Equations of Ballistics.—Clemmow, p. 343. Reproduction of Print for the Blind.—Allen, p. 463.

- Photoelectrograph for the Blind.—Perls: Thomas, p. 174.
 The Optical Electrical Transformation of Printed Matter into Sound or Raised Characters for the Blind, with the help of the "Principle of Optical Congruence."—Schutkowski, p. 344.
 Reading Print by Photocell [Photoelectrograph and Visagraph for the Blind].—Walker, p. 174.
 A Method for the Investigation of the Impedance of the Human Body to an Alternating Current.—Brazier, p. 581.
 Some Remarks on the Question of the Resistance of the Body to High-Frequency Currents.—Malov, p. 581.
 The International Organisation of Broadcasting.—Brenot, p. 232.
 Brush Discharge in Air affects Engine Performance, p. 581.

- Brush Discharge in Air affects Engine Performance, p. 581 : see
- also X-Rays. A Portable Amplifying Electro-Cardiograph.—Sien.ens Company, p. 117.
- p. 117.
 An Electrical Calculating Machine.—Mallock, p. 460.
 The Work of the Institute for the Applications of Calculation [including Problems connected with Oscillation Transformers, Thermionic Currents, etc.], p. 580.
 Improvements in Prytherch's Capacity Dilatometer.—Haughton and Adcock: Prytherch, p. 519.
 Small Capacity Changes: see also Kathetron, Ultra-micrometric.
 A New System of Multiple Telegraphy by Carrier Current [including the "Amplifilter"].—Kajii and Matsumae, p. 166.
 Carrier in Cable [and the Use of a New Type of Amplifier embodying the Principle of "Negative Feedback."]—Clark and Kendall p. 628.

- p. 628.
- Report on the Tests in the Punkwa Caves and Tunnels .- Fritsch,

- Report on the sets in the Funkwa Caves and Tunners.—Frisch, p. 558.
 On the Classification of Technical Papers [The Brussels Decimal Classification System].—Moench, p. 231.
 The Transparency of Clouds and Fogs to Visible and Infra-Red Radiations.—Müller, Theissing and Kiessig, p. 55.
 An Electron-Tube Time-Delay Relay for Automatic Stopping of Coll-Making Machines for Valve Filaments.—Holloway, p. 640.
- An Electron-Tube Time-Delay Relay for Automatic Stopping of Coil-Making Machines for Valve Filaments.—Holloway, p. 640. Glow Tube Checks Over- and Under-Voltages [for Testing Coin Relays in Coin Collectors], p. 117. The Method of Coincidences, or a Quick Method of Determining the Approximate Value of a Simple Correlation Coefficient.—Savur, p. 287. Code of Fair Competition for the Radio Manufacturing Industry [submitted to the National Recovery Administration], p. 640. International Electricity Congress, Paris, 1932: Summaries of Papers in Sections I and II, p. 55. Radio-Electricity at the International Electrical Congress, Paris, 1932 [Summaries], p. 115. The Biological Effect of Cosmic Rays.—Lakhovsky: Rivera, p. 117. Curre Sheet for Working out Measurements of complex Quantities.

- Hermann, p. 461. The 8th " Deutsche Physiker- und Mathematikertag," Bad Nauheim, 1932, p. 232.
- Radio International [a Five-Language Dictionary giving 900 of the Most Important and Commonly Used Radio Terms].—Pariser,
- p. 640. Development and Programme of the Differential Analyser.—Bush, p. 231. A Simple Method for the Numerical Solution of Differential Equa-
- tions: Note on Error and its Avoidance.—Bickley, p. 461. Successive Approximations [to the Solution of Linear Differential Equations] by the Rayleigh-Ritz Variation Method.—MacDonald,
- p. 461. The Potential Value in Industry of Discoveries which are of Com-

- The Potential Value in Industry of Discoveries which are of Com-paratively Small Scientific Importance.—Moore, p. 55. Dissemination of Scientific Knowledge.—Leifson, p. 231. Signal Distortion in Telegraph Circuits.—Jolley, p. 238. The Measurement of Telegraph Distortion.—Terry, p. 462. Mutual Impedance of Grounded Wires Lying On or Above the Surface of the Earth.—Foster, p. 640. A Study of Stray Earth Currents [from D.C. Lines] and of Electro-lutio Decorrence. Schlumbarger, p. 117.
- A study of stray Earth currents [non D.C. Eness] and of Electro-lytic Phenomena.—Schlumberger, p. 117. Table of Organisation and Programme of Higher Education in Electrical Engineering in Different Countries, p. 231. Applied Science Not So Efficient as Supposed : Overall Efficiency of Automobile Transportation of Passengers only 3%.—Winston,
- p. 405. The Permanent Electret.—Eguchi, p. 232. Electrical Communication in 1932.—I. T. and T. Laboratories, etc.,
- p. 288.
- New Applications and the Expansion of Recent Uses of Electricity: Recent Applications of Electrical Methods.—Sills: Bishop, p. 231.
 Some Recent Developments in Electromagnetic Inspection and Test
- Some Recent Developments in Encourse and Source States and Source Sources for Industrial Control.—Gulliksen, p. 232. Electronic Devices for Industrial Laboratory.—Sharp, p. 117.

- Electronic Devices for Industrial Cohordon.—Commisci, p. 202. Electronic Devices in a Testing Laboratory.—Sharp, p. 117. Electron-Physics [Review of Progress].—Campbell, p. 461. Greatly Enhanced Effects of Galvanic Electrotherapy by use of High Voltages.—Pasteur, p. 344. Ellipsoidal Functions and Their Application to Some Wave Problems.
- —Hanson, p. 580. Notes on Relations between Elliptic Integrals and Schlomilch Series [in connection with the Calculation of Modulation Products].— Bennett, p. 519.

Miscellaneous.

- The E.M.Fs developed by Man in Contact with a Metallic Conductor [and Their Diurnal Variation].—Vles and others, p. 463 : see also Growth.
- also Gröwth.
 Tests on High-Speed Diesel Engines by Electrical [Piezoelectric, Ultra-Micrometric, etc.] Methods.—Nägel, p. 232.
 The Strobophonometer [for Studying the Knock in Internal Com-bustion Engines].—Stansfield and Carpenter, p. 55.
 The Physical Society's Exhibition, January, 1933, pp. 232, 287
- and 288.
- What the Industry brings to the Berlin Radio Exhibition, p. 580. Wireless and Other Electrical Apparatus at the German Aircraft Exhibition, 1932, p. 115.
- From the Great German Radio Exhibition, Berlin, 1932.-Burstyn, p. 115.
- Technical Advances at Radio Exhibition, Berlin, 1932 [especially

- Superhetrodyne Receivers], p. 115. The 9th German Radio Exhibition, 1932, p. 55. Olympia, 1932: Impressions of the Radio Exhibition, p. 115. This Year's Radio Exhibition (Olympia).—Turner, p. 115. The Post Office Exhibit at the National Radio Exhibition.—Morri -Morris,
- The Post Office Exhibit at the National Radio Exhibition.—Morris, p. 115.
 Artificial Fever: see also Heating, Radiothermy, Ultra-Short.
 Investigations of the Transparency to Light of Fog.—Born, Dziobek and Wolff, p. 581.
 Remark on the Paper by G. Köhler and A. Walther: On the Fourier Analysis of Functions with Discontinuities, Corners and Similar Peculiarities.—Feinberg, p. 230.
 The Theory of Functions and Its Application in Engineering. Rothe, Ollendorff and Pohlnausen, p. 55.
 The Contribution of Radiotelegraphy to Geophysics, p. 382.
 Progress in 1932 in the Work of the German State Post Office, n. 405.

p. 405.

- p. 405.
 Glossary of Physical Terminology.—Weld, p. 640.
 Researches on the Influence of Electrical Conditions on the Growth of Infants.—Vies, p. 174: see also E.M.Fs.
 Short Wave H.F. Currents. Their Heating Effects—Short Wave Diathermy.—Cross, p. 117.
 A Study of High-Frequency Heating [in connection with the Production of Artificial Fever].—De Watt: Whitney, p. 117.
 The Theory of Heating by Induced H.F. Currents.—Ribaud, n. 231
- p. 231.
- p. 201. High-Frequency Heating in Industry, p. 117. Heating : see also Electrotherapy, Fever, Radiothermy, Ultra-Short. Meeting of the Heinrich-Hertz Institute, 1933, p. 640. The Electrostatic Production of High Voltage for Nuclear Investiga-tions.—Van de Graaff, Compton and Van Atta, p. 462. The International Indexing of Scientific and Technical Papers.—
- Bradford, p. 287.
- An Installation for Telephony on Infra-Red Rays.-Fernandes, p. 640.
- D. Orv. Infra-Red, The Next Playground of Vacuum Tubes [Sextant, Locating Aeroplanes by Heat of Exhaust, Warships by Funnel Heat, Icoberg Warning].—Macneil, p. 117. Infra-Red Fog-Eye picks up Ships below Horizon.—Macneil,
- p. 581.
- p. 391.
 International Instruction in Communication.—Gill: Craemer, Ebeling and Küpfnüller, p. 287.
 Inductive Interference from Fault Currents on E.H.T. Power Lines.—Jackman, p. 519.
 The Production of 4 800 000 Volt Hydrogen Ions,—Livingston and Lawrence p. 489.

- The Production of 4 800 000 Voit Hydrogen Ions,—Livingston and Lawrence, p. 462. The Juridical Control of Radio in France.—Mestre, p. 287. The Kathetron as a Detector of Small Capacity Changes [Application to Detection of Foreign Bodies or Flaws].—Craig, p. 344. "Radio Knife" employing Induced Currents [thus dispensing with Electric Cord Connection], p. 231. Lamé, Mathieu and Related Functions in Physics and Engineering.—

- Lamé, Mathieu and Related Functions in Physics and Engineering.— Strutt, p. 461.
 Variation of Luminous Intensity of Incandescent Lamps as a Function of Variation of Applied Voltage.—Pécheux, p. 231.
 Notes on the Method of Least Squares.—Eddington, p. 287.
 On the Theory of Errors and Least Squares.—Jeffreys, p. 55.
 An Electronic Phase-Failure Relay [for Lifts or Hoists driven by Polyphase Mains].—Stanbury and Brown, p. 344.
 The Atoms as a Source of Light [and the Search for "Cold " Light]. —Dushman, p. 344.
 Electrodeless Discharge and Sources of Monochromatic Light.— Esclangon, p. 232.

- Electrodeless Discharge and Sources of Monochromatic Light.— Esclangon, p. 232.
 A Sonic Nephelometer [for Comparison of Light transmitted by Translucent Materials].—Wilson, p. 462.
 On Linear Systems with First-Order Partial Derivatives with Two Variables.—Carleman, p. 639.
 Looking Ahead as 1933 Opens, p. 231.
 Loud Speakers summon Physicians in the New York Hospital ["Doctors' Paging Service"], p. 463.
 Limiting Values of Vectors of a Locus Curve [Application to the Simple Calculation of Maxima and Minima in place of Differential Calculus].—Kind, p. 580.
- Simple calculation of maxima and minima in place of Distriction Calculus].—Kind, p. 580. Mechanical Models for Electrical Processes.—Weller, p. 580. German State Railways' Apparatus for the Calibration of Measuring Instruments for the Determining of Mechanical Movements.— Bernhard and Kammerer, p. 288.

- An Example of a Complete Analogy between Electrical and Mechanical Oscillation.—Ramsauer, pp. 500-501. Elimination of the Troubles in Telephone Circuits produced by Mercury-Vapour Rectifiers.—Collett, p. 518. Removal of Metallic Deposits (on Walls of Discharge Tubes) by High-Frequency Currents.—Robertson and Clapp, p. 640. Development of the High-Frequency Metallurgical Oven.—Tama, p. 344
- p. 344. Partial Sterilisation of Milk in Continuous Process, by Use of Magnetostriction Generator.-Gaines, p. 174.
- Adio-Telephony in Mines, —Noack, p. 231. A Photoelectric Method of Putting in Evidence the Mitogenetic Radiation of Gurwitsch.—Petri: Gurwitsch, p. 288.

- Kadiation of Gurwitsch. —Petri: Gurwitsch, p. 288.
 Tuning In on Mosquitoes, p. 117.
 Mosquitoes attracted by Ultra-Violet Lamps and then Trapped or Electrocuted, p. 581.
 Variable Speed Motor with Vacuum Tubes.—Alexanderson, p. 640.
 Optical Manograph with Low Inertia for Study of Internal Com-bustion Motors].—Serruys, p. 463.
 Modern Communication Systems including Multiple Utilisation of Transmission Systems, as in Two-Band Telephone Systems and Simultaneous Telephony and Telegraphy on Short Waves]. —Litchen n 116. -Lüschen, p. 116.
- and Simultaneous Telephony and Telegraphy on Short Waves]. -Lüschen, p. 116.
 Mutual Impedance of Grounded Wires for Horizontally Stratified Two-Layer Earth.-Riordan and Sunde, p. 624.
 Mutual Induction between Power and Telephone Lines under Trans-ient Conditions.-Radley and Josephs, p. 462.
 Radio Tubes Amplify and Measure Nerve Messages.-Bronk, p. 117. A Universal Precision Stimulator [Thyratron Circuit for Nerve Physiology Researches].-Schmitt, p. 174.
 Radio and Electrical Nomenclature [a Plea for a General "Cleaning Up"].-Scroggie, p. 462.
 Optical Telephony to a Ship Below the Horizon, p. 463.
 Optico-Electrostatics [Optical Method of Determining the Electric Field in a Dielectric].-Tutumi, p. 174.
 Engineering Organisation.-Shea, p. 580.
 The New German Patent and Trade Mark Law.-Neumann, p. 117.
 The U.S.A. Patent "Pool," p. 231.
 Patent Problems in the Field of Electronics [and the Need of Careful Study of Previous Patents].-Toulmin, p. 117.
 Changes in Patent Procedure, p. 117.
 An Extremely Simple Method of Periodogram Analysis.-Alter, p. 343.

- p. 343. Application of Periodogram Analysis .-- Sandström : Practical
- Lindquist, p. 405. The Use of the Selenium Barrier-Layer Photocell for Physical Measurements.—Bergmann, p. 116. The Importance of the Barrier-Layer Photocell in Illuminating
- Engineering.—Bloch, p. 232. Colour Measurement by the Three-Colour Method using a Photocell.
- -Bloch, p. 344. Semi-Conductor Photocells and Their Application in Colorimetry and Photometry.-Lange, p. 344. Control of Wood-Pulp Cooking by Photocell.-Navarre Paper Mills,

- Control of Wood-Pulp Cooking by Photocell.—Pavarre raper muse, p. 482. Making Measurements with the Photocell.—Walker, p. 581. Photocell Applications:—Surgeon and Operating Theatre Door; Mine Door opened by Mine Locomotive; Drinking Fountain; Theatre Admission Checking; Comparing "Amount of Ink in Printing Book Forms for Uniformity, p. 640. Photocell signals when Coffee is roasted to Correct Shade, p. 463. New Use for Photocell [preventing Damage to Printing Machinery if Paper Breakage occurs], p. 288. Photocell Control against Paper Breakage in Newspaper Printing, p. 581.

- Inducter Conveyor operated by Photocell, p. 581.
 Laundry Conveyor operated by Photocell, p. 581.
 Photocell ensurce Perfect Jig-Saws, p. 581.
 Colour Matching in Automobile Plant (by Photocells : for Parts finished in Different Places or Other Factories), p. 581.
 Light Sensitive Process Control (Photoelectric Control of Concentration of Solutions).—Alfriend, p. 640.
 Photoelectric Scopometer (for Turbidimetric and Colorimetric Measurements).—Bausch and Lomb Company, p. 344.
 A [Photoelectric] Smoke Density Meter.—Bean, p. 231.
 A Protocelestric Meter Two Photometers, using Barrier-Layer Photocells.—Bergmann, p. 344.
 A Practical Photoelectric Relation Meter [using the Bergmann Selenium Barrier-Layer Photocell].—Bergmann, p. 462.
 Improvement of the Photoelectric Polarimeter.—Bruhat and Guinier, p. 288. p. 288.
- Experiments on Polarimetry by Photoelectric Technique : Measure-ments of the Rotatory Dispersions of Some Sugars.—Bruhat and Chatelain, p. 232. A Photographic Recording Photoelectric Densitometer.—De Vore,
- p. 640. The Exact Measurement of Photographic Densities [by Photo-
- electric Methods].—Fleury and Boutry, p. 462. Photoelectric Transparency Meter.—Geffcken and Richter, А
- A New [Barrier-Layer] Photoelectric Microphotometer with Syn-chronous Recording Equipment.—Lange, p. 116. An Improved Photoelectric Recorder.—La Pierre, p. 581.

Miscellaneous.

- Experiments with a Recording Photoelectric Pyrometer [and Its Use as an Automatic Control in Spot Welding, etc.].—Müller and Zetzmann, p. 344.
 Photoelectric Colour-Measuring Instruments.—Neustadt, p. 519.
 Photoelectric Compensation Method for Photometric Measurements [using Two Selenium Barrier-Layer Cells].—Richter, p. 116.
 A Photoelectric Instrument for Company, p. 462.
 The Limiting Magnitude observable with a Photoelectric Stellar Photometer. The Application of a Thermionic Amplifier to the Photometry of Stars.—Sinclair Smith : Whitford, p. 462.
 Measurement of Yarn Thickness and Evenness [by Photoelectric of the Photometry of Stars.—Sinclair Smith : Whitford, p. 462.
 Measurement of Yarn Thickness and Evenness [by Photoelectric of the Spectrum.—WestingHouse Company, p. 116.
 An Integrating [Photoelectric] Photometer for X-Ray Crystal Analysis.—Wheeler Robinson, p. 581.
 The Development of Commercial Photoelectric Every watches Bowling, Rivet, and Valve-Stem Heaters : of Amount of Chlorine introduced into Water Supply, p. 581.
 Cloth-Dyeing Machine with Photoelectric Reverser : Electric Eye watches Bowling, Alley "Foul Line" : Smoke Recorder and Truck-Height Indicator in Holland Tunnel, p. 231.
 Photoelectric Photometer tests Air Purity, p. 463.
 Photoelectric Photometer tests Air Purity, p. 463.
 Photoelectric Photometer using a Photoelectric Cell.—Boutry, p. 462. Experiments with a Recording Photoelectric Pyrometer [and Its Use as an Automatic Control in Spot Welding, etc.].-Müller

- p. 462.
- P. too.
 The Posophotometer [Photographic Exposure Meter using Photo-electric Cell].—Établissements Filmograph, p. 581.
 The Measurement of Very Weak Luminous Flux by means of a Photoelectric Cell.—Gambetta, p. 462.
 The Automatic Control of Street Lighting by Photoelectric Cells.—
- Hauser, p. 116.
- The Synchronoscope, using a Photoelectric Cell.—Heyne, p. 462. The Automatic Timing of the Ostwald Viscometer by means of a Photoelectric Cell [eliminating Psychological Errors].—Jones and Talley, p. 519.
- Use of the Photoelectric Cell in Biology [Study of Area and Shape of
- Blood Cells.—Savage, p. 231. Applications of Photoelectric Cells in Chemical Engineering.— Smithells, p. 288. Photoelectric Cells: Their Properties and Uses. II. Some

- Photoelectric Cells: Iner Properties and Uses. 11. Solie Applications.—Stoolley, p. 463. Photoelectric Cells in Photometry.—Walsh, p. 581. The Bernheim Photoelectric Cell requiring No Amplification, p. 519. Rotations of Fricticaless Steam or Gas Meter counted by Photoelectric Cell, p. 463.
- Photoelectric Cell Applications [Control of Hydrogen Ion Concen-tration in Various Processes · Handling of Hot Steel Strip in Tube Manufacture], p. 344. Stringent Test for Photoelectric Cell [Half-Mile Optical Link in Broadcast Transmission], p. 271. Testing of Raw Silks for Uniformity of Thread Diameter by Photo-electric Cell p. 213
- Photoelectric Coll p. 117.
 Photoelectric Coll p. 117.
 Photoelectric Coll p. 117.
 Photoelectric Control of Paper Cutter for Paper Bag Making.— Shoults, p. 463.

- Photoelectric Control in the Printing Arts [with List of Sixteen Applications to Printing, Publishing, etc.], p. 116. Photoelectric Control of Works Lighting saves 4 000 kwh Monthly,
- Photoelectric control of works Lighting saves 400 kWH Moltany, reduces Lamp Replacements 25%, improves Production and reduces Accidents, p. 344.
 Photoelectric Relays.—King, p. 174.
 Photophony [Photo-Telephony] with Voltage Modulation of Incandescent Lamp—Viewed from Its Wave Form.—Suzuki, 2021
- p. 231.
- p. 231.
 Opposed Photronic Cells responsive, independent of General Illumination, p. 344.
 Report on the Publications Questionnaire Sent to Members of the American Physical Society [Economy Proposals: the Abstracts Problem], p. 287 ; see also Abstracts.
 The Activities of the Physikalisch-Technische Reichsanstalt in the Year 1931, p. 232.
 Recording and Measuring Blood Pressure by a Piezoelectric Method. —Bugnard, Gley and Langevin, p. 231.
 The Use of Piezoelectric Crystals in Resonant Oscillation for the Measurement of Pressures [New Piezoelectric Dynamometer]. —Guerbilsky, p. 580.

- -Guerbilsky, p. 580.
- The Piezoelectric Measurement of Mechanical Vibrations, Accelerations and Extensions.—Kluge and Linckh, p. 288. Piezoelectric Methods of Measuring Mechanical Forces.-
- -SaxI :
- Prezoelectric Methods of Measuring Mechanical Forces.—Saki: Kluge and Linckh, p. 117.
 Piezoelectric Measurement of Pressures [e.g. in Large Guns, or Very Low Pressures] and Weights.—Weber, p. 463.
 Piezoelectric : see also Engines, Motors, Pressure, Vibrations, Vibrometer, and under "Measurements and Standards."
- Pittsburgh's Contributions to Radio.-Kintner : Fessenden, p. 232.

- On Some Processes of Electro-Culture and on the Distant Action of Metallic Circuits on the Growth of Plants,-Failletaz : Lakhovsky, p. 117.
- Plants as Detectors [Rectifying Effect of Sap Movement].--Marinesco p. 174.
- p. 174.
 Decreasing the Tractive Force necessary for Ploughing by the use of Electric Currents between Plough and Blade.—Weber, p. 344.
 [Variation of] Conductivity of NaCl Crystals under Pressure.— Gyulai, p. 463.
 Direct Determination of the Mean Pressure in Heat Engines.—
- Labarthe, p. 580. Methods of Measuring and Recording Rapidly Varying Pressures [as in Aeroplane Engine Cylinders: a Photoelectric Method]. —Labarthe and Demontvignier, p. 231. On the Use of the Pentode Valve for Pressure Recording in Fluids.—

- On the Use of the Pentode Valve for Pressure Recording in Fluids.— Oliphant, p. 161. Measuring Instantaneous Pressure in Shot Guns [Piezoelectric Gauge], p. 117. The Principles of Electromagnetism.—Moullin, pp. 462 and 519. The Concepts of Inverse Probability and Fiducial Probability Referring to Unknown Parameters.—Fisher : Jeffreys, p. 287. Probability Statistics, and the Theory of Errors.—Jeffreys, p. 287. Probability Theory and Telephone Transmission Engineering.— Hoyt, p. 230. Electromagnetic-Wave Progneting in the U.S.S.R.—Petrowsky.
- Electromagnetic-Wave Prospecting in the U.S.S.R .- Petrowsky, p. 519.
- Modern Methods of Protection against Theft by Automatic Alarm Apparatus [Infra-Red-Ray, Vibration, and Capacity-Change Methods].—Dubois, p. 640.

- Methods).—Dubois, p. 640. Publicity and the Physicist.—Potter, p. 580. The Movements of a Quartz Crystal in an Electrostatic Field.— de Gramont, p. 518. The Rotation of a Quartz Crystal.—de Gramont, p. 581. On the Probable Emission of a Radiation of Small Penetrating Power from Certain Metals.—Reboul, p. 463. Highly Absorbable Radiations from "Resistance Cells."—Reboul,
- 463.
- p. 463. The Radio Corporation of America and Its Ramifications.—Winkler,
- Radio Engineering.—Terman, pp. 288 and 519. Survey of the Most Important Developments in Radio Engineering and Acoustics in 1932.—Elektrotechnischer Verein, p. 580.
- and Acoustics in 1932.—Elektrotechnischer Verein, p. 580. Radio Engineering Handbook.—Edited by Henney, p. 462. The Radio Industry in 1932 [Some Statistics], p. 405. The Technical Problems of Radio-Telephony, at the U.I.R. Meeting at Montreux, June, 1932.—Adam, p. 55. Radio-Telephony [Survey for 1932, including the "Compandor" Device].—Faulkner, p. 230. Radiothermy [including Artificial Fever : with Bibliography].— Whitney n. 117

- Whitney, p. 117. On a New Type of Reasoning and Some of Its Possible Consequences and Remarks on the Preceding Note on Many-Valued Truths,—
- Zwicky : Bell, p. 519. Some Electrical Methods of Remote Indication.—Midworth and Tagg, p. 580. Remote Indication and Control Devices.-Tagg, p. 462.
- Utilising the Results of Fundamental Research in the Communica-tion Field.—Jewett, p. 287. Research Developments in 1931 and 1932.—Koenemann, p. 405.

- Research Developments in 1931 and 1932.—Koenemann, p. 405.
 Recent Radio Research, p. 232.
 Electronics in Resistor Manufacturing.—Podolsky, p. 640.
 The Dielectric Constant [of Rocks containing Salt and Bitumen] at Volkenroda.—Löwy, p. 640.
 Royal Society Conversazione—Radio and Other Exhibits, p. 580.
 Variation of Conductivity of Rubber impregnated with Lamp Black: Applications to Variable Resistance, Vibrometer, Pick-up, Tuning Fork, etc.—Granier, p. 405.
 Progress of Vulcanisation watched by means of Oscillator Grid-Circuit Condenser Plates embedded in Rubber Mass, p. 640.
 On the Prior Probability in the Theory of Sampling.—Jeffreys, p. 230.
- p. 230.

- bort-Wave Treatment of Nervous Paralysis.—Kellner, p. 463.
 Short-Wave Wireless Communication.—Ladner and Stoner, p. 580.
 Skin Effect with Direct Current.—Weber, p. 519.
 Iron Tube filled with Metallic Sodium as Overhead Conductor for Large Currents.—Boundy, p. 519.
 The Projection of Solid Images in Space by the "Katascope."—
- Siemens Company, p. 640. The Rôle of Statistical Method in Economic Standardisation.—Shew-
- hart, p. 519. The Distribution of Second Order Moment Statistics in a Normal System.—Wishart and Bartlett, p. 55. Principles of Statistical Analysis Occasionally Overlooked.—McNish,
- p. 499. The Nitriding of Steel by the use of High-Frequency Currents,
- p. 117, Stroboscopy applied to the Calibration of Electricity Meters .-
- Maurer, p. 640. Le Roy's Generalisation of Borel's Method of Summation of Divergent Series : the Theory of the Product of Two Series.— Vignaux, p. 405.

Miscellaneous

- Summation Methods in Smoothing Curves.—Vercelli, p. 405. Tangential Polar Coordinates or Polar Coordinates, and Their Applications.—Jacob, p. 461. On Writing Technical Articles.—Williamson, p. 462. Determining the Transmission Efficiency of Telegraph Circuits.— Jolley, p. 462. An All-Mains, Voice Frequency Single-Channel High Speed Duplex Telegraph System Owen and Bevis n. 116.

- An All-Mains, Voice Frequency Single-Channel High Speed Duplex Telegraph System.—Owen and Bevis, p. 116.
 Point to Point Radio Telegraphy : Present Position and Possible Future Development.—Wells, p. 116.
 Ten Years of Wireless, 1922–1982.—The First Ten Years of the "Société des Amis de la T.S.F." and of the Journal "L'Onde Électrique."—Gutton, p. 343.
 Nikola Tesla and His Work, p. 288.
 The Application of Radio Technique to the Testing of Materials : the Measurement of the Internal Friction of Metals.—Polotowsky, p. 581
- In the interstitution of the internal relation of internals, p. 581.
 Electron Tubes in Radio City Theatres: Lighting-Control, Sound, and Air-Conditioning Applications of Tubes, p. 344.
 Magnetic Apparatus for the Measurement of Thicknesses [e.g. of Thin Sheets or Wires of Non-Magnetic Materials: Direct-Reading, suitable for Continuous Operation].—Bricout, p. 288.
 On the Relation by Fourier's Integral in the Solution of Transient
- Solution by Fourier's Integral in the Solution of Transient Phenomena.—Nukiyama, p. 639. The Robot Translator [the Caralozzi Translatorphone], p. 344. Trends in Radio Design and Manufacturing [Binaural Transmission : Hill-and-Dale Gramophone Recording : Reflex Circuits : "etc.],

- p. 580. Photoelectric Cell Equipment in Steel Tube Works, p. 344. The Rôle of Vacuum Tubes in a Tube Factory.—Koechel, p. 581. Thyratron Control of Welding in Tube Manufacture.—Lord and
- Livingston, p. 640. The Siccometer: an Ultra-Micrometer for the Testing of Moisture in the Manufacture of Paper.—Carsten and Walter: Siemens

- The Manufacture of Paper.—Carsten and Walter: Siemens & Halske, p. 232.
 The [Ultra-Micrometric] Measurement of Small Electrodynamic Forces with the Condenser Microphone.—Agricola, p. 223.
 Ultra-Micrometric Measuring the Temperature of Metal Container in Calorimetric Processes.—Esser and Grass p. 519.
 The Sounding String as a Measuring Apparatus [as Ultra-Micrometric Device for Small Movements in Buildings, Hulls, etc., and Lathe Investigations].—Haake, p. 232.
 A Non-Electric Ultra-Micrometric Device for Measuring Length-or Pressure-Changes, depending on Mercury Columns of Large and Small Cross-Sections.—Mohr, p. 55.
 Ultra-Micrometric : see also Capacity, Electromagnetic, Engines, Kathetron, Mechanical, Motors, Rubber, Thicknesses.
 The Production of the Merget Phenomenon [Gaseous Thermodifusion] by d'Arsonvalisation by Ultra-Short Waves.—Bordier, p. 23.
- p. 231

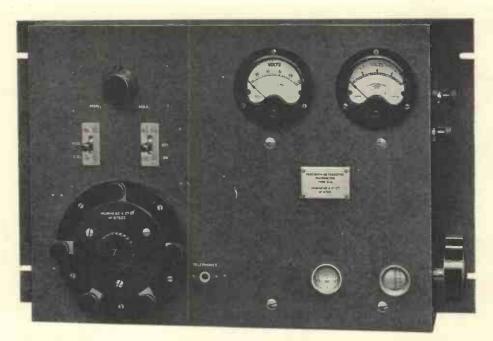
- p. 231.
 [Ultra-Short] Radio Waves Kill Insect Pests [in Wheat, Seeds, Tobacco, Vegetables, etc.].—Davis, p. 463.
 The Ultra-Short Electromagnetic Waves, with particular regard to Military Applications.—Gatta, p. 519.
 Experimental Researches on the Effects of Ultra-Short Waves on the Functioning of the Cerebellum.—Gemelli, p. 463.
 Measurements of the Temperature in the Interior of an Egg in the Electric Field of Ultra-Short Waves.—Jellinek, p. 463.
 Heating Effects of Ultra-Short Waves.—McLennan, p. 344.
 Ultra-Short Electric Waves : a New Development in Diathermy.—
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- Schliephake, p. 640.

- Killing Weevils in Wheat by [Ultra-] Short Wave .--- Westinghouse Company, p. 463. Ultra-Short [6 Metre] Waves kill Pests in Stored Beans, Peas, etc.,
- p. 640.
- Ultra-Short Waves [as used for producing Artificial Fever] bake
- Ultra-Short Waves las used for producing Artificial Fever] bake Crustless Bread, p. 640. Ultra-Short: see also Fever, Heating. New Valves and Their Industrial Applications [Special Pliotrons, Cathode-Ray Tubes for X-Ray Analysis, Thyratrons, and Phanotrons].—Hull, p. 174: see also Coil-Making, Electronic, United Ultra-Ultra-Phanotrons.—Hull, p. 174 : see also Coil-Making, Electronic, Weighing, Wheat. Polar Chart Makes Vector Addition Easy.—Arapakis, p. 174. Measurement of Velocity of Projectiles by means of Kerr Cell.— Cranz, Kutterer and Schardin, p. 232. Measuring the Vibrations of Machine Parts [by Method of Tuned

- Reeds) to Reduce Noise and Speed-Up Production.—Firestone, Durbin and Abbott, p. 55. Mechanical Vibration Research.—Den Hartog, p. 55. Measurement of the Dissipation of Vibratory Energy in a Steel Bar by an Electrical Method.—Kimball, p. 232.
- Measurement of the Vibrations of Railway Superstructures .- Koch,
- p. 288. Mechanical Vibration of Conductor due to D.C. Corona Discharge.

- Mechanical Vibration of Conductor due to D.C. Corona Discharge. —Kumagai and Nagaya, p. 518. The Technique of Vibration Measurement [Survey with Biblio-graphy of 73 Items].—Lehr, p. 55. Magnetostriction of a Circularly Magnetised Bar and Its Applica-tions [e.g. to Investigate the Torsional Vibrations of a Rotating Shaft].—Mori, p. 50. The Vibration of Taut Electric Wires [and the Avoidance of Reson-ance Effects].—Respighi, p. 117. The Investigation of Mechanical Vibrations by Phase Measurement. —Späth. p. 232.
- -Späth, p. 232. The Employment of the Reciprocity Relations in the Investigation
- of Mechanical Vibrations.—Steinheil, p. 232. Torsional Vibrations in Axles and Shafts and the Resonance Oscilla-
- tions in Filters [Suggestion of a Method of Testing].-Treves, p. 232.
- Suggested Unit of Vibration Amplitude [the "Pal"].-Zeller, p. 463.
- Portable Vibration-Velocity Meter for Velocities from 25 to 2 500 Mils per Second through Frequency Range 25 to 5 000 Cycles/

- Second, p. 344.
 Vibrometer: see also Piezoelectric, Rubber.
 Moving Track for Walking Exercises, with Speed Controlled by Walking Speed through Thyratrons and Photocells or Condenser Effect.—British Thomson-Houston Company, p. 117.
 Lightning Research [and Water Divining Tests].—Rudenberg:
 Lehmann, p. 55.
- Automatic Weighing with Vacuum Tubes [for Wind Tunnel Measure-
- ments of Aeroplane Stresses, etc.].—Eastman, p. 344. The Use of a Condenser-Resistance Combination as Timing Circuit
- for Grid-Controlled Rectifiers used in Welding, p. 581. Valve Method of Measuring the Moisture Content of Wheat-Hartig and Sullivan, p. 581.
- Hartig and Sullivan, p. 881. Study of the Wing Beats of a Bird or Insect by the use of a Hot Wire and Cathode Ray Oscillograph.—Magnan, p. 581. Notes on Wireless History.—Taylor, p. 232. X-Rays Ionise at 100 Feet [and the Possibility of using such Distant Ionising Action for "Short-Circuiting Aeroplane Engines"].— Du Mond, p. 405 : see also Brush Discharge.



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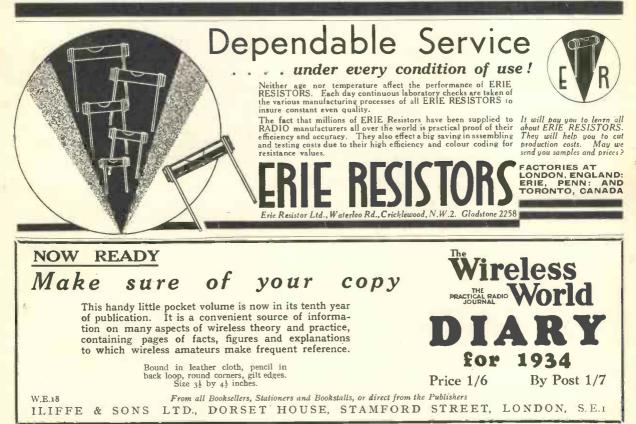
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