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# Wireless World 

Electronics, Television, Radio, Audio

Sixtieth year of publication


Our cover picture this month, which might be called "two kinds of digits', shows a five-by-seven array of light-emitting diodes made by Standard Telecommunications Laboratories. Display devices are discussed on page 444.

## IN OUR NEXT ISSUE

The first of a series of articles on the elements of linear i.cs

Constructional details of a 100 -watt quality amplifier

Review of some of the latest techniques in domestic sound and television receivers

September 1970
Volume 76 Number 1419

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## The I.C. Industry-who will pick up the bits?

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When Dr. F. E. Jones, managing director of Mullard Ltd, Britain's largest manufacturer of integrated circuits, admits that his company is losing £1M per year on i.c. production and says that he "cannot see his way through the dense undergrowth of the i.c. world" it is time for us all to sit up and take notice. In particular the Government should heed his words for if it does not Britain's integrated circuit industry will be doomed.

The problem is simply one of price. Take for example one of the simple integrated circuits, the t.t.l., quad, two-input gate. This device requires 28 separate manufacturing processes and consists of a chip of silicon about 1.5 mm square containing 24 components, four of which are transistors. At the beginning of 1969 the selling price of this device was 15 s 6 d , by the end of the year it had fallen to 5 s 6 d but, at the present time, it must be marketed at between 1s 2 d and 1 s 8 d -which is well below manufacturing costs-in order to compete with American concerns.

How can the Americans sell at this price in the U.K. when Dr. Jones has said that he cannot see any way to produce the circuit for this sort of money now, or in one year's time or even five years' time no matter what production methods are used?

The Americans, of course, have a huge home market, most of which is a closed shop to outsiders because of the "Buy American Act". During 1969 this market absorbed 413.4M integrated circuits, of which about 342 M were digital. In the same period the U.K. produced only 12 M integrated circuits. Also the Americans have a huge investment in the Far East where they employ 20,000 to 30,000 workers. It would appear that the silicon chips are made in America and sent by air to the Far East where they are assembled into packages by workers paid about 8 d per hour.

If the finished products are taken back to the U.S. for distribution, tax is paid only on the added value. But what is the difference in value between a processed silicon chip and the same chip in a package? Because of the difficulty in assessing this added value the amount paid in tax could be negligible. When asked if the U.K. could not mount such an "offshore" operation to their advantage Dr. Jones said that the cost savings produced in this way would be nullified by our own import duty which is based on the selling price and not the added value. Even taking into account the obvious advantages the Americans have Dr. Jones said that he still could not see how they achieved such a low price.

It is obvious that either the Americans are selling off their surplus production in this country or they are making a deliberate attempt to undermine our own integrated circuit industry. The thought is frightening when one considers all the industries which employ integrated circuits and would therefore have to rely entirely on American sources of supply.

Before the Americans can be accused of dumping it has to be proved that they are selling components at a price which is lower than in the country of origin. But what is the country of origin when the various processes are carried out in different parts of the world?

If British-component manufacturers wish to export to America they have to prove to the American excise authority, before the goods are shipped, that the price takes into account shipping costs and is not less than the price in this country. British manufacturers have no such protection where American goods are concerned. They cannot go on sustaining such huge losses and prompt action is needed from the Government in the form of import controls if the integrated circuit industry is to survive.

In view of the gravity of this threat to the U.K. semiconductor industry, and indeed the whole of the electronics industry, it is surprising that no reference is made to the prevailing situation in the latest "statistical survey" of the industry issued by the Electronics "Little Neddy" on the day Dr. Jones made his announcement.

## Phase-locked Stereo Decoder

# Improved channel separation and low distortion obtained using an inductorless circuit 

by R. T. Portus*, A.M.I.E.E. and A. J. Haywood*, A.M.I.E.E.

During a stereo broadcast the f.m. carrier transmitted by the B.B.C. is composed of three parts, as shown in Fig. 1. The components are:

1. Left plus right $(\mathrm{L}+\mathrm{R})$ forming the compatible mono signal containing frequencies up to 15 kHz .
2. Left minus right ( $\mathrm{L}-\mathrm{R}$ ) which amplitude modulates a 38 kHz carrier. (The carrier is suppressed to better than $1 \%$ in order to make full use of the maximum deviation available at the transmitter.)
3. A low level "pilot tone" at half the carrier frequency, i.e. at 19 kHz , whose zero crossing points are coincident with those of alternate cycles of the 38 kHz suppressed subcarrier. This tone is used as a reference to regenerate the suppressed subcarrier at the receiver.

## Stereo decoders

There are many forms of decoders, ${ }^{1}$ the most popular being the switching type where the 19 kHz pilot tone is filtered by a tuned circuit, frequency doubled (to 38 kHz ) and used to switch the complex signal-as shown in Fig. 2. Appendix III explains why complete channel separation is not achieved by such simple switching.

## Limitations of tuned-circuit decoders

Poor separation results if the derived 38 kHz switching signal is modulated by any extraneous signal. This means that all the stereo information has to be removed by the tuned circuit. Also, if the output from the 19 kHz tuned amplifier contains any frequencies which pass through subharmonics of 38 kHz , the frequency multiplication stage will produce a modulation of the recovered 38 kHz . This in turn will produce sum and difference frequencies ("birdies") when switching the incoming


Fig. 1. Frequency spectrum of a stereo multiplex signal.


Fig. 2. Block diagram of switching stereo decoder.
complex signal. From the above considerations it may be seen that a high- $Q$ tuned circuit is required. On the other hand, if the $Q$ is made very large the phase of the recovered subcarrier becomes extremely drift sensitive. Any change in phase will reduce the separation. The effect of uncompensated phase error on separation is as follows.

| Phase error <br> at 19 kHz (deg.) | Separation <br> (dB) |
| :---: | :---: |
| 1 | 82.5 |
| $2 \frac{1}{2}$ | 54.5 |
| 5 | 42 |
| 10 | 30 |
| 15 | 23 |

Fig. 3 shows the change for small changes in tuned circuit $L$ or $C$ with various values of $Q$.

## Phase-locked decoder

Because of the shortcomings of tuned decoders the authors decided to use a phase locked loop to regenerate the 38 kHz suppressed subcarrier. A phase-locked loop is used to lock a locally generated signal in phase with an input signal whose frequency is liable to vary. Such a system may be given a very narrow bandwidth so that noise components of the input signal will not affect the loop operation.

If a locally generated 38 kHz signal is binary divided the remaining 19 kHz may be phase locked to the "pilot tone". This means that alternate zero crossings of the 38 kHz signal are coincident with those of the 19 kHz pilot tone. The locally generated 38 kHz signal is therefore in phase with the suppressed subcarrier.
The performance of such a system may be made superior to that of decoders using tuned circuits for the following reasons: 1. A phase-locked oscillator is a closed-loop


Fig. 3. Phase changes due to variation of $L$ or $C$ in a parallel tuned circuit.
system and so changes in component values, due to ageing, temperature etc., are corrected. Other systems have no comparison between input and output, and so errors may only be reduced by careful matching, the use of high quality components and accurate setting up.
2. The generation of "birdies" is very much reduced because the loop is given a low bandwidth, ensuring that phase modulation of the 38 kHz switching signal can only occur at low frequencies.
3. The setting up of a phase-locked loop is a simple matter, a d.c. voltmeter being the only instrument used. For other decoders an oscilloscope is usually required.

## Performance of phase-locked decoder

The decoder (British patent application No. 35600/69) was tested using a Radiometer stereo signal generator, and the following specification obtained.

| Frequency | Separation |
| ---: | :---: |
| 80 Hz | 28 dB |
| 1 kHz | 45 dB |
| 10 kHz | 40 dB |

In a decoder fitted with a variable matrix the separation was 56 dB at 1 kHz .

Distortion at 1 kHz and with full modulation is $0.3 \%$ (predominantly 2 nd harmonic), and the distortion introduced by crosstalk at 1 kHz is 67 dB down at full modulation. The mono and stereo gains are within 1 dB of each other. Cancellation is 45 dB . The input voltage range is 130 mV r.m.s. to 1.3 V r.m.s., and the output voltage 250 mV r.m.s.

The separation at 80 Hz could be improved by using matched components in the p.s.d. stage, but directional information is negligible at this frequency so that component matching is hardly worthwhile.

## Operation of a phase-locked loop

The phase-locked loop (Fig. 4) can be looked upon as a servo-amplifier in which the 19 kHz pilot tone is used as an input reference phase, and the servo loop used to control a local oscillator in a fixed phase relationship. If there is a fixed phase between two signals then they must be at the same frequency. A phase-locked subcarrier may be regenerated by deriving the 19 kHz from 38 kHz by use of a binary divider. Alternate zero crossings of the 38 kHz signal are therefore held locked to the incoming 19 kHz .
The operation of the loop is as follows. The balanced phase sensitive detector (p.s.d.) produces a d.c. output proportional to the difference in phase between the input frequency $\left(f_{\text {in }}\right)$ and a locally derived frequency ( $f_{o}$ ), plus higher frequency components produced by the chopping of the input signal. For a balanced p.s.d. the lowest frequency present is that produced by the highest audio frequency ( 15 kHz ) beating with the 19 kHz chopping signal. The difference signal is $4 \mathrm{kHz}(19 \mathrm{kHz}-15 \mathrm{kHz})$. This error signal is then amplified and low pass filtered by the error amplifier. The filtering removes the high frequency signals produced by the balanced modulator. The error amplifier output is used to control a voltage controlled oscillator (v.c.o.).

If the p.s.d. is not perfectly balanced small low-frequency audio signals will be present at the p.s.d. output. If the frequency of these signals approaches the loop bandwidth they will not be completely filtered out by the error amplifier. The resulting "ripple" on the error amplifier output will cause "jitter" on the v.c.o. output (i.e. phase modulation).

Loop operation is such that a change in phase between ( $f_{\text {in }}$ and $f_{o}$ (e.g. due to drift)


Fig. 4. Block diagram of phase-locked loop.


Fig. 5. Complete stereo decoder system built round the phase-locked loop.
causes the output of the p.s.d. to drive the v.c.o. in such a direction as to hold the phase of $f_{\text {in }}$ locked to that of $f_{o}$.

The system behaves as a servo-loop with a bandwidth determined by the time constant of the filter in the error amplifier.
When deciding on loop bandwidth two points have to be considered. These are "jitter" on the v.c.o. and the time required to pull into lock. The first point is important because phase jitter will reduce channel separation. Jitter is minimized by having a low loop bandwidth.

On the other hand if loop bandwidth is made too small the loop will take a long time to pull into lock.

A compromise must therefore be made and a bandwidth of 25 Hz was found to be adequate.

Theory and design equations for the loop are given in appendices I and II.

## Practical decoder system

In Fig. 5 the pre-amplifier acts as a buffer on the tuner output. Its gain is made variable so that a fixed level of pilot tone is presented to the loop independent of the tuner output level.

The phase detector is balanced, and the error amplifier is made differential in order to maintain balance. The output from the error amplifier constitutes the control voltage of the voltage controlled oscillator (v.c.o.) which is free running at approximately 76 kHz .

By the use of binary dividers square-wave outputs are obtained at 38 kHz and 19 kHz . The former output drives the decoding transistors and the latter the loop p.s.d. transistors. The decoder outputs are matrixed and de-emphasized to provide the left and right channel outputs.

On acquiring lock an output is obtained from the in-phase detector. This output is amplified and filtered, and used to allow decoding to begin, and to drive a stereo indicator lamp, if required.

## Circuit description

The complete decoder circuitry is shown in Fig. 6. $T r_{1}$ and $T r_{2}$ comprise a pre-amplifier whose output level is adjusted by $R V_{1}$ to set the p.s.d. gain constant. The p.s.d. consists
of $R_{5}, R_{7}, T r_{3}$ and $T r_{4}$, and these transistors are used in the inverted mode to minimize offset voltage. Since the bases of $\mathrm{Tr}_{3}$ and $T r_{4}$ are driven alternately at 19 kHz the p.s.d. and differential error amplifier $I C_{1}$ form a double-sideband suppressed-carrier modulator, the output of which is modified by the error amplifier response.
Audio signals close to the loop bandwidth are attenuated by $C_{3}$. The phase shift due to $C_{3}\left(10_{2}^{1 \circ}\right)$ is corrected for in the matrix which is fully described in a later section.

The error amplifier $I C_{1}$, type U6E7709393 or similar, is a low cost differential inteintegrated operational amplifier. This is chosen for its high gain and low input offset voltage. At $\pm 6 \mathrm{~V}$ supply the typical open loop gain is 72 dB .
$C_{4}$ and $C_{6}$ provide an additional h.f. rolloff beyond the loop unity gain frequency so that loop stability is not affected.
The amplifier response is tailored to give an overall loop bandwidth of 25 Hz with an error response damping factor of 0.707 . The d.c. gain is chosen from a consideration of the static error due to v.c.o. drift. The error is $<1^{\circ}$ at 19 kHz .
$R V_{2}$ provides an adjustment for input offset voltage, which would otherwise appear as a phase error. The low input offset voltage temperature drift of $I C_{1}$ ensures good phase stability.
The v.c.o. ( $T_{6}$ and $T r_{7}$ ) is a conventional astable multivibrator with the timing voltage of the bases controlled by $I C_{1}$. It is arranged to free run at approximately $76 \mathrm{kHz} . R V_{4}$ provides a fine frequency control by adjustment of the mark/space ratio.
$R_{25}$ and $D_{1}$ ensure that the v.c.o: will not operate above 80 kHz , by clamping the error amplifier input to approximately +0.6 V .

The 76 kHz signal is then applied to $I C_{2}$ which is a dual D-type SN7474 or similar binary divider. $I C_{2}$ will then provide a 38 kHz and a 19 kHz switching signal with a $1: 1 \mathrm{mark} / \mathrm{space}$ ratio. The 19 kHz signal is applied to the loop p.s.d. transistors $\mathrm{Tr}_{3}$ and $T r_{4}$, thus closing the loop. The 38 kHz signal is applied to the decoding transistors $T r_{11}$ and $T r_{12}$.

The bases of all the switching transistors are pulled negative to remove stored charge and to hold the transistors off in the presence of audio signals.


Fig. 6. Circuit diagram of decoder. Integrated circuits $I C_{1}$ and $I C_{3}$ are type U6E770 9393 or equivalent, and $I C_{2}$ type SN7474N or equivalent. Transistors can be BC108 or equivalent for $n-p-n$ types, and ZTX 500 or equivalent for $p-n-p$. Diodes are IS44 or equivalent. Resistors can be $\frac{1}{4} W 5 \%$ tolerance unless specified otherwise.

The action of $D_{2}, D_{3}$ is to speed up lock-in at switch-on for outputs greater than $\pm 0.6 \mathrm{~V}$. The diodes shunt current away from $C_{10}$ and effectively increase loop bandwidth. Between $\pm 0.6 \mathrm{~V}$ the diodes have no effect.

In-phase detector. Transistor $\boldsymbol{T r}_{10}$ is driven by both binary dividers so that it is off for $\frac{1}{4}$ cycle only of the 19 kHz . Thus a pulsed d.c. component is produced when the loop is locked. This signal is filtered and amplified by $I C_{3}$ and used for the following purposes: 1. To turn on a stereo indicator lamp, if required.
2. To allow decoding to begin in $\operatorname{Tr}_{11}$ and $T r_{12}$. If the decoder is allowed to switch during mono transmission, supersonic noise around 38 kHz will be heterodyned into the audio bandwidth causing a deterioration in $\mathrm{s} / \mathrm{n}$ ratio. Also from some transmitters a 23 kHz low-level tone is present during mono transmission. This tone would produce a "beat" at 15 kHz in a free running decoder. For this reason the v.c.o. is not

Fig. 7. Oscillograms of typical waveforms generated by the locked-loop.


Upper: pilot tone $+150 \mathrm{~Hz}(A=B)$. Lower: emitter of $\mathrm{Tr}_{3}$.


Upper: 19 kHz binary output. Lower: 38 kHz binary output.


Upper: $\operatorname{Tr}_{10}$ base drive.
Lower: $\operatorname{Tr}_{10}$ emitter.


Matrixing of $15 \mathrm{kHz} \operatorname{signal}(A=B)$. No de-emphasis. Pilot omitted.


Matrixing of 1.5 kHz signal $(A=B)$.
No de-emphasis. Pilot tone omitted.


As above with 19 kHz pilot tone included.
allowed to operate above 80 kHz , i.e. the binary output cannot exceed 20 kHz .
3. To ensure that the l.h. and r.h. channels do not reverse in the presence of noise etc. If the loop initially locks in the wrong direction i.e. 1.h. and r.h. channels are reversed, a positive output will be produced by the in-phase detector, $T r$, will be turned on thus clearing the binaries, and reversing 1.h. and r.h. This will also be the case if a line transient flips one binary only. In the writers' experience the loop has never locked in the wrong direction. Typical waveforms of the loop in operation are given in Fig. 7.
4. To keep the mono and stereo gains approximately constant via $\operatorname{Tr}_{5}$.

Matrix. Once the signal has been decoded by $T r_{11}$ and $T r_{12}$ it is matrixed and deemphasized via $T r_{14}$ and $T r_{15}$. Matrixing is necessary in any switching decoder as may be seen from the theory given in appendix III.

Power supply. The circuit of Fig. 6 is shown for a supply of $\pm 6 \mathrm{~V}$. Fig. 8(a) shows a suitable low cost regulator using a miniature mains transformer.

Single supply operation is accomplished from an unregulated ( 15 V minimum) supply by altering the "earth" rail from the 0 V to the -6 V line as shown in Fig. 8(b).

In this case there are two minor circuit alterations: capacitor $C_{1}$ is reversed; and resistors $R_{52}$ and $R_{58}$ are returned to the former -6 V rail i.e. instead of the former 0 V rail. The signal "earth" line becomes, of course, the former -6 V line.

## Setting up procedure

The decoder is set up using a d.c. voltmeter The stages are as follows:

1. With no input signal adjust $R V_{2}$ and $R V_{3}$ for 0 V at test points $\mathrm{TP}_{1}$ and $\mathrm{TP}_{2}$ respectively.
2. Apply a stereo signal and adjust $R V_{1}$ until a negative voltage 1.5 V appear at $T P_{2}$ (Adjust $R V_{4}$ if necessary).
3. Adjust $R V_{4}$ to bring $\mathrm{TP}_{1}$ back to zero.
4. Adjust $R V_{1}$ to bring $\mathrm{TP}_{2}$ to -1.5 V .

## Operation

Several decoders have been built and tested by the authors, using both single and dual supply operation.
Over the last year they have proved to be


Fig.8. Decoder power supply arrangements. (a) Stabilized supply for $\pm 6$ V. (b) Supply obtained from an unregulated 15 V (or greater) d.c. source.
reliable and have required no adjustment beyond the initial setting up procedure.
The high inherent separation, in particular at high frequencies, produces a marked improvement in performance over that obtained with more conventional decoders.

## Notes

This decoder design arose from work done on a phase-locked loop frequency multiplier made to improve the resolution of an engine tachometer.

The authors are grateful to J. W. Hill and D. L. Lynas for the use of equipment and for helpful criticism, and thank Rolls-Royce Ltd for permission to publish.

A kit of parts including a printed circuit board is available, mail order only from Integrex Ltd, P.O. Box 45, Derby, DE1 1TW. The price is $£ 819 \mathrm{~s} 6 \mathrm{~d}$ plus 2 s 6 d for carriage and packing. This printed circuit board is adapted to single or dual supply options. The size of the board is $100 \mathrm{~mm} \times 125 \mathrm{~mm}$ (approx.) and it may be seen from the photograph that a high packing density has been achieved. To simplify assembly, component positions have been marked and the track is roller tinned. A power supply kit is also available.

## REFERENCE

1. "Receiving Stereo Broadcasts", Wireless World, September 1966.


Decoder components mounted on a printed circuit board approximately $100 \mathrm{~mm} \times 125 \mathrm{~mm}$.

## Appendix I

## Loop Theory

The constants used are defined as follows:
$K_{d}=$ phase detector gain constant in volts/radian.
$K_{o}=$ v.c.o. gain constant in radians $/ \mathrm{s} / \mathrm{V}$ $(=2 \times \mathrm{Hz} / \mathrm{V})$.
$G(s)=$ error amplifier transfer function
$\theta_{\text {in }}=$ input reference phase angle.
$\theta_{o}=$ locally generated phase angle
$\theta_{e}=$ phase angle error $\left(=\theta_{\text {in }}-\theta_{o}\right)$.
The loop block diagram is redrawn below.


The integration term ( $1 / s$ ) is introduced by the conversion of the frequency of the v.c.o. to its phase.

By inspection of the diagram
$\frac{\theta_{o}}{\theta_{i n}}=\frac{K_{o} K_{d} G(s) 1 / s}{1+K_{o} K_{d} G(s) 1 / s}=\frac{K_{o} K_{d} G(s)}{s+K_{o} K_{d} G(s)}$
The error amplifier has a response that can be shown to be

$$
\begin{equation*}
G(s)=\frac{A\left(1+s T_{2}\right)}{1+s\left(T_{1}+T_{2}\right)} \tag{2}
\end{equation*}
$$

where

$$
A=\frac{R_{1}}{R_{3}} ; \quad T_{1}=C R_{1} ; \quad T_{2}=C R_{2}
$$

Substituting (2) in (1) we get

$$
\begin{equation*}
\frac{\theta_{o}}{\theta_{\text {in }}}=\frac{\left[K_{o} K_{d} A /\left(T_{1}+T_{2}\right)\right]\left(1+s T_{2}\right)}{s^{2}+\frac{s K_{o} K_{d} A T_{2}}{T_{1}+T_{2}}+\frac{K_{o} K_{d} A}{T_{1}+T_{2}}} \tag{3}
\end{equation*}
$$

Where it is assumed $K_{0} K_{d} A T_{2} \gg 1$.
This is of the form

$$
\begin{equation*}
\frac{\theta_{o}}{\theta_{i n}}=\frac{2 \eta \omega_{n} s+\omega_{n}{ }^{2}}{s^{2}+2 \eta \omega_{n} s+\omega_{n}{ }^{2}} \tag{-6V}
\end{equation*}
$$

where using servo terminology $\omega_{n}=$ natural (undamped) frequency of the loop and $\eta=$ loop damping factor.

$$
\text { Thus } \begin{align*}
\omega_{n} & =\left(\frac{K_{0} K_{d} A}{T_{1}+T_{2}}\right)^{\ddagger}  \tag{4}\\
\eta & =\frac{T_{2}}{2}\left(\frac{K_{0} K_{d} A}{T_{1}+T_{2}}\right)^{\frac{1}{2}}=\frac{T_{2}}{2} \omega_{n} \tag{5}
\end{align*}
$$

## Static phase errors

Since the phase loop contains an integrator term then the steady state phase error will be reduced to zero if the v.c.o. free-running frequency is the same as that of the input frequency.
The response of the loop to a disturbance causing drift in the v.c.o. free running frequency can be obtained from the figure below.

where
$\omega_{\text {v.c..o. }}=$ free running v.c.o. frequency $\omega_{o}=$ disturbance (or drift) frequency.
It can be seen that

$$
\begin{equation*}
\frac{\omega_{\text {v.c. } 0}}{\omega_{o}}=\frac{1 / s . K_{o} K_{d} G(s)}{1+1 / s \cdot K_{o} K_{d} G(s)} \tag{6}
\end{equation*}
$$

By referring $\omega_{\text {v.c.. }}$ back to an equivalent $\theta_{e}$ we get
$\frac{\theta_{e}}{\omega_{o}}=\frac{1 / s}{1+1 / s K_{o} \cdot K_{d} \cdot G(s)}=\frac{1}{s+K_{o} K_{d} G(s)}(7)$
For a step input of $\omega_{o}=\Delta \omega_{o}$ then

$$
\begin{equation*}
\theta_{e} \cdot s=\frac{\Delta \omega_{o}}{s} \cdot \frac{1}{s+K_{o} K_{d} G(s)} \tag{8}
\end{equation*}
$$

Applying the final value theorem we get
steady state phase error $=\frac{\Delta \omega_{o}}{K_{o} K_{d} A}$

$$
\begin{equation*}
(\text { since } G(0)=A) \tag{9}
\end{equation*}
$$

This phase error is required in order to pull the v.c.o. away from its free-running frequency. By making $K_{o} K_{d} A$ sufficiently large the phase error can be made as small as required.

For those who wish to pursue phaselocked loop theory a very good account is given in "Phaselock Technique" by Floyd M. Gardner, published by John Wiley and Sons Inc.

## Appendix II

## Loop equation constants

P.S.D. gain constant. For a phase error $\gamma$, when the loop is locked the mean output voltage from the phase detector, $V_{o}$, is given by:
$V_{o}=\frac{V_{i n}}{\pi} \int_{\frac{\pi}{2}+\gamma}^{\frac{3 \pi}{2}+\gamma} \sin \theta \mathrm{d} \theta$
where $V_{\text {in }} \sin \theta$ is the input signal.
Thus $\left|V_{o}\right| \approx \frac{2}{\pi} \times V_{i n} \times \gamma$ where $\gamma$ is small.
Thus, if we choose an input signal of 200 mV
peak to peak amplitude:

$$
K_{d}=63.7 \mathrm{mV} / \mathrm{radian}
$$

or

$$
K_{d}=63.7 \times 10^{-3} \mathrm{~V} / \text { radian }
$$

Steady state error. From equation (9) it may be seen that the steady state error is given by:

$$
\text { Error }=\frac{\Delta \omega_{o}}{K_{o} K_{d} A}
$$

where $\Delta \omega_{o}$ is the frequency difference of the free running v.c.o. and the pilot signal, $K_{d}$ is the phase detector gain constant and $K_{o}$ is the v.c.o. gain constant.
Now
$K_{d}=63.7 \times 10^{-3} \mathrm{~V} / \mathrm{rad}$ and
$K_{o}=1.2 \times 10^{3} \times 2 \pi \mathrm{rad} / \mathrm{s} / \mathrm{V}$ (measured)
For the v.c.o., the frequency drift is approx. $0.075 \% /{ }^{\circ} \mathrm{C}$. It follows that for a steady state error of $1^{\circ}$ over $20^{\circ} \mathrm{C}$ temperature change.

$$
A=214
$$

From equation (4)

$$
\omega_{n}=\frac{K_{o} K_{d} A}{T_{1}+T_{2}} \quad T_{1}+T_{2}=4.16 \mathrm{~s}
$$

From equation (5)

$$
\eta=\frac{T_{2} \omega_{n}}{2} \therefore \quad T_{2}=9 \mathrm{~ms}
$$

## Appendix III

## Matrixing in switching decoders

In an f.m. stereo broadcast the instantaneous deviation of the transmitter is given as :

$$
\begin{gathered}
f=0 \cdot 9\left[\frac{1}{2}(\mathrm{~A}+\mathrm{B})+\frac{1}{2}(\mathrm{~A}-\mathrm{B}) \sin \omega_{s} t\right. \\
\left.+0.1 \sin \frac{\omega_{s}}{2} t\right]
\end{gathered}
$$

where $\frac{\omega_{s}}{2 \pi}=38 \mathrm{kHz}$
The pilot tone is $0.1 \sin \frac{\omega_{s}}{2} t$.
In a switching decoder the input signal is treated as if it were time division multiplexed. The signal is multiplied by a square wave:

$$
=\left(\frac{1}{2}+\frac{2}{\pi} \sin \omega_{s} t+\frac{2}{3 \pi} \sin \omega_{s} t+\ldots\right)
$$

Suppose there is phase error $\phi$ existing between the 38 kHz carrier used for modulation and the local 38 kHz decoding signal.

The output signal will be proportional to $V_{1}$ where:

$$
\begin{aligned}
V_{1}= & {\left[(\mathrm{A}+\mathrm{B})+(\mathrm{A}-\mathrm{B}) \sin \omega_{s} t\right] } \\
& {\left[\frac{1}{2}+\frac{2}{\pi} \sin \left(\omega_{s} t+\phi\right)\right.} \\
& \left.+\frac{2}{3 \pi} \sin \left(3 \omega_{s} t+\phi\right)+\cdots\right] \\
& \left(\text { neglecting } \sin \frac{\omega_{s}}{2} t\right)
\end{aligned}
$$

$$
=\left(\frac{1}{2}+\frac{1}{\pi} \cos \phi\right) \mathrm{A}+\left(\frac{1}{2}-\frac{1}{\pi} \cos \phi\right) \mathrm{B}
$$

plus modulation
around $\omega_{5} 3 \omega_{5}$ etc, which is of the form:

$$
V_{1} \propto(\mathrm{~A}+\Delta \mathrm{B})
$$

where $\Delta$ is dependent on the phase shift $\phi$.
If the decoding signal is shifted by $180^{\circ}$, the output signal may be shown to be proportional to $V_{2}$ where: $V_{2} \propto(\mathrm{~B}+\Delta \mathrm{A})$.
The purpose of matrixing is to subtract $\Delta V_{2}$ from $V_{1}$ and vice-versa.

$$
\text { i.e. } \begin{aligned}
V_{1}-\Delta V_{2} & \propto \mathrm{~A}+\Delta \mathrm{B}-\Delta \mathrm{B}-\Delta \Delta \mathrm{A} \\
& \propto \mathrm{~A}-\Delta \Delta \mathrm{A}
\end{aligned}
$$

It may be seen that signals from channel A only are present in one output and from channel B in the other.
Thus, if the phase shift $\phi$ is known, and hence $\Delta$, complete separation of an ideal broadcast is achieved.

## Announcements

A lecture on the British Trans-Arctic Expedition $1968 / 69$ will be given by Sqn. Ldr. F. W. Church. D. J. Collins and R. G. Shears at a meeting of the R.S.G.B. at 18.30 on 28 th September at the I.E.E., Savoy Place, London w.C.2.

A post-graduate evening course of sixteen meetings entitled "Integrated Circuit Electronics" will be held at North East London Polytechnic, Romford Road, London E. 15. beginning 22nd October. Fee $£ 4$.
"Single Standard Colour Television Receivers" is the title of a 6 -week course of evening lectures to be held at Norwood Technical College, Knight's Hill, London S.E.27, commencing 20th October. Fee $£ 1$.

Basic Electronics is the subject of two ten-evening courses comprising lectures and practical work to be held at Twickenham College of Technology, commencing 15th October and 21 st January. Further details from The Principal, Twickenham College of Technology, Egerton Road, Twickenham, Middx. Fee 5 gn per course.
A course in Modern Sound Studio Techniques is to be held through the winter at the Northern Polytechnic, Holloway Road, London N.7. Sessions will be on Thursday evenings beginning 29th October. The fee for the fifteen sessions is 6 gn .

The scope of the annual Manchester exhibition of measuring equipment is to be extended next year to include professional-grade products in three main groups: electronic equipment, electronic components and apparatus for industrial measurement and control. The show will be held at the City Hall, Deansgate, from 5th to 8th October, 1971. Organizers: Industrial Exhibitions Ltd, 9 Argyll Street, London WiV 2HA.

Following the acquisition of Painton \& Co., of Northampton, by the Plessey Co., the Resistor and Connector Divisions of Plessey have combined with Painton in whose name the business will in future be conducted with R. W. Addie continuing as managing director. Painton now have four operating divisions, three commercial-connectors, resistors and exports-and one production.

# Television Wobbulator 

## 2. Circuit Details

by W. T. Cocking, F.I.E.E.

In last month's article the general principles of a wobbulator specially designed for the alignment of television i.f. amplifiers were discussed. The complete circuit diagram of the instrument is shown in Figs. 1 and 2. The heart of it is the section labelled "Wobbly Oscillator" with the transistor $T r_{2}$. This is an h.f. type operating as a Colpitt's oscillator.

The inductor is $L_{1}$ connected between the collector and the earth line, which is the positive of the $17-\mathrm{V}$ power supply. The base is earthed for r.f. through the $1-\mathrm{nF}$ capacitor $C_{5}$ and the capacitors $C_{7}$ and $C_{6}$, of 6.8 pF and 82 pF respectively, are between collector and base with the emitter joined to their
junction. These two form the split capacitance of a Colpitt's oscillator. The tuning capacitance proper comprises $D_{2}$ in series with $C_{8}, D_{2}$ being the varactor diode the capacitance of which is varied by a $50-\mathrm{Hz}$ voltage applied through $R_{9}$. The purpose of $C_{8}$ is merely to prevent $L_{1}$ from shorting $D_{2}$ at 50 Hz .

The emitter resistor $R_{8}$ completes the d.c. path of $T r_{2}$ but allows the emitter to be free at radio frequency. It is effectively in shunt with the base-emitter path of the transistor. The other resistor $R_{7}$ and the zener diode $Z_{1}$ give a stabilized supply of some 12 V for the oscillator.

Wound in bifilar fashion with $L_{1}$ is $L_{2}$
which feeds the diode $D_{1}$ with load $R_{3}$ returned to a potential divider $R_{1}, R_{2}$ across the $17-\mathrm{V}$ supply. The diode load capacitance is $C_{2}$ with a filter $R_{4}, C_{3}$. The rectified output of the diode is positive-going and is applied in series with the small bias voltage from the potential divider to the base of $T r_{1}$ which acts as a d.c. amplifier with emitter resistance $R_{6}$. Its collector is joined to the base of $T r_{2}$ and fed through $R_{5}$. In Fig. 1, this stage is labelled a.a.c, for automatic amplitude control, and it forms a kind of a.g.c. system whose purpose is to minimize variations of the amplitude of oscillation of $T r_{2}$ as its frequency is varied.

If, for any reason, the amplitude increases


Fig. 1. Complete circuit diagram of the wobbulator, apart from the power supply. $\operatorname{Tr}_{2}$ generates a signal varying in frequency between 30.5MHz and 42.5 MHz which is fed to the amplifier under test through the attenuator controlled by $S_{1} . \operatorname{Tr}_{3}$ is the wave shaper which enables a linear relation between frequency and displacement on the c.r.o. to be obtained.
the rectified output of $D_{1}$ increases and $T r_{1}$ passes more current. Consequently the voltage drop across $R_{5}$ increases and the base-emitter voltage of $T r_{1}$ is reduced and this reduces the amplitude of oscillation. The net result is to reduce the magnitude of any changes in the amplitude of oscillation.

The output of the oscillator is taken from the single-turn coil $L_{3}$ coupled to $L_{1}$ and connected to the r.f. attenuator. This comprises a ladder network of resistors with a single-pole 6-way switch $S_{1}$. When terminated at the output socket by $75 \Omega$ this network has a constant impedance of $37.5 \Omega$ at the switch arm for any position of the switch and, because of $R_{28}$, a constant impedance of $75 \Omega$ is presented to the coupling coil $L_{3}$. The actual impedance is slightly different because $R_{28}$ actually has the standard value of $39 \Omega$. Further, resistor tolerances in the network affect the impedance relations slightly.

Viewed from the output socket the impedance varies with the switch position, but the variation is appreciable only between the full output and the next-to-full output positions. This is inevitable with a simple ladder attenuator. The attenuator is intended merely to adjust the output to the required level in steps of about 5 dB . It is not intended to provide precisely equal and known steps; that would entail a more elaborate construction and the use of precision resistors.

The total attenuation available is not more than some 30 dB . More may be needed with some i.f. amplifiers and it is recommended
that any such extra attenuation be provided externally. For this purpose, the Belling-Lee coaxial attenuators type L729 are particularly convenient and two 6-dB types (L729/6) and one 12-dB (L729/12) in conjunction with the internal attenuator should be sufficient for almost any amplifier.

We now come to the wave shaper, $\mathrm{Tr}_{3}$. It was explained in Part 1 that the relation between the frequency generated by the oscillator and the voltage applied to the varactor diode $D_{2}$ is logarithmic and that to obtain a linear relation between frequency and the X-deflection voltage of the oscilloscope it is necessary for the voltage applied to $D_{2}$ to have an exponential relation to the deflecting voltage. This exponential relation
is provided by $\mathrm{Tr}_{3}$.
A BF177 transistor is used. This is primarily intended for use as a video output stage and is rated for operation at 100 V . It is used here on a $70-\mathrm{V}$ supply, its collector being taken to earth (positive) through $R_{11}$ of $220 \mathrm{k} \Omega$ and its collector voltage being fed to $D_{2}$ through $R_{9}$ and $R_{10}$ of $330 \mathrm{k} \Omega$ each. The emitter is returned to the negative of the $70-\mathrm{V}$ supply. The collector potential with respect to earth can thus vary from zero (collector current cut-off) to almost -70 V (bottoming).

The varactor diode $D_{2}$ is rated for a maximum of 60 V . The application to it of a higher voltage is thus dangerous to its life and as it is an expensive component it is

Fig. 2. Circuit diagram of the power supply. Two transformers are used since the requirements are then met by stock-item components.


8 -way cable to wobbulator


Top of the circuit board showing the placement of components.


Underview of the circuit board.
important to protect it from the accidental application of anything more than 60 V . The protective device comprises the diode $D_{3}$ with $R_{12}$ and the two zener diodes $Z_{2}$ and $Z_{3}$. The zener diodes keep the anode of $D_{3}$ at $51 \mathrm{~V}( \pm 5 \%)$ negative to the earth line irrespective of variations of the supply voltage or the tolerance of $R_{12}$.

As long as the junction of $R_{9}$ and $R_{10}$ is less negative to earth than this $D_{2}$ is non-conductive and has no effect. When the junction becomes slightly more negative than the zener voltage $D_{2}$ conducts and clamps the junction of $R_{9}$ and $R_{10}$ at about 0.7 V more than the voltage across $Z_{2}$ and $Z_{3}$. Even if $T r_{3}$ is bottomed, therefore, the voltage applied to $D_{2}$ is limited to 54.35 V , allowing for 0.8 V drop across $D_{3}$ and for $5 \%$ high tolerance on the zener diodes. Two zener diodes in series are used instead of a single one to reduce the dissipation per diode. It is thought that this should reduce the risk of a diode going open-circuit, for that would put the protective circuit out of action.

The d.c. bias for $\mathrm{Tr}_{3}$ comes from the $70-\mathrm{V}$ supply. A stabilized supply of 18 V is first derived from $R_{19}$ and $Z_{4}$. A variable voltage of 13.3 V to 18 V is available from the slider of the "Coarse mid-band frequency control" $R_{20}$. Roughly $1 / 20$ of this voltage is applied to the base of $\operatorname{Tr}_{3}$ by a potential divider comprising $R_{14}$ and the network $R_{15}, R_{16}$ and $R_{17}$, the last of which is variable to form a "Fine mid-band frequency control". This is essential when the equipment is used to provide a narrow-band sweep for soundchannel alignment. It is not essential with the wide-band sweep for vision channel use, but even then it is convenient.

A $7-\mathrm{V}, 50-\mathrm{Hz}$, supply from a mains
transformer is applied through a phasereversing switch $S_{4}, S_{5}$ to a potential divider $R_{22}, R_{24}$. The maximum voltage available from $R_{22}$ is 0.48 V r.m.s. and roughly $1 / 10$ of this is applied to the base of $\mathrm{Tr}_{3}$ through the potential divider $R_{14}, R_{18}$. The voltage actually applied to the transistor is thus variable from zero to a maximum of about 130 mV peak-to-peak. For the narrow sweep for the sound channel $S_{\overline{3}}$ connects $39 \Omega$ in shunt with $R_{22}$, and this reduces all voltages to about $1 / 12$.

Another $7-\mathrm{V}, 50-\mathrm{Hz}$, supply provides the X-deflection voltage for the oscilloscope. It is reduced to about 1.63 V r.m.s. by $R_{26}$, $R_{27}$; this is about 4.7V peak-to-peak. It is sufficient with the oscilloscope used to give an X-trace of about two-thirds of the screen width and the X -expansion control on the oscilloscope permits the length of trace to be increased beyond this as desired. If the oscilloscope used does not have such a control, then $R_{26}, R_{27}$ should be replaced by a variable potentiometer. Of course, if the oscilloscope used needs more than some 20 V p-p for full X-deflection, a higher supply than 7V r.m.s. must be provided.

The voltage across $R_{27}$ is applied through a simple variable integrator $R_{25}$ and $C_{9}$ to provide an X-deflection voltage which is lagging in phase on the input, the phase being adjustable by $R_{25}$. This is necessary to correct for phase shift in the Y -deflection circuits. This occurs mainly in the wave shaper and is caused principally by $C_{8}$ with $R_{9}$ and $R_{10}$. Some also may occur in the receiver under test, especially if the output from it is taken from a video stage. The capacitance of $D_{3}$ also has an effect and, indeed, the addition of only 10 pF across $D_{3}$ produces a noticeable phase shift. This may seem surprising in view of the frequency of 50 Hz , for few realize how sensitive circuits


## Interior of the marker oscillator.

## are to phase shift.

It is important to keep stray capacitance low in the collector circuit of $\mathrm{Tr}_{3}$, for the waveform is not sinusoidal and so a phase shift introduced here cannot be completely corrected. It is found in practice that the residual error can be no more than the thickness of the trace on the c.r.t., which is quite adequate for all normal requirements.

This is the basic wobbulator. On one half-cycle of the sine-wave deflection the oscillator frequency varies from 30.5 MHz to 42.5 MHz , or such smaller range as may be set. On the next half-cycle it varies from 42.5 MHz to 30.5 MHz and, of course, the X -deflection varies in the opposite direction.

The traces for increasing frequency and for decreasing superpose to give a single visible trace only if the X and Y channels have the same phase shift and only if the
i.f. amplifier gives the same response to increasing and decreasing frequencies. The latter does not necessarily occur, and it will not if the sweep repetition rate is too great in relation to the bandwidth of the amplifier. With wideband amplifiers, such as television amplifiers, the effect is unlikely to be observed with a $50-\mathrm{Hz}$ sweep except, possibly, at the troughs introduced outside the passband by high- $Q$ trap circuits. Even there, however, they have not so far been observed.

It is essential to have at least one marker on the oscilloscope trace to indicate frequency and it is a convenience to have two markers. An internal marker oscillator is provided and is $\operatorname{Tr}_{4}$. Its circuit is substantially the same as that of the wobbly oscillator, but it is tuned by an ordinary variable capacitor $C_{15}$ of 27 pF . It operates at 6.2 V from a supply stabilized by $Z_{5}$. It is built into a screening box, the zener diode and $R_{41}$ being outside it to reduce the total dissipation within the box and so the temperature rise within it. The output is taken from a 2 -turn coil $L_{8}$ through a $100-\Omega$ resistor $R_{46}$ and thence by a twisted pair of wires to $S_{2}$ and to $L_{5}$ or $R_{47}$. The earthy lead from $L_{8}$ is earthed at one point only, close to where it emerges from the screening box of the marker oscillator. This is important.

A socket for an input from a signal generator is provided on the front panel and is connected by a pair of twisted wires to $L_{6}$. The only earth point is that of the coaxial socket on the front panel. Again, this is important.

With the marker system used here it is desirable that r.f. from the signal generator
or from the internal marker oscillator should not reach the input of the i.f. amplifier. Unless each coupling circuit is earthed at one point only, it has been found impossible to prevent greatly excessive leakage. Even with the single-point earthing, there is still some leakage and with the marker amplitude control turned right down traces of the markers are visible on the screen. They are not at all troublesome in normal usage, however.

The internal marker oscillator has a second use. When $S_{2}$ connects $R_{46}$ to $R_{47}$ the output is connected to $L_{3}$ and so to the input of the attenuator. It is thus mixed directly with the output of the wobbly oscillator. The switches $S_{2}$ to $S_{5}$ are ganged together; they are actually a rotary switch wafer having 4 -poles, each 2 -way. When $S_{2}$ connects the marker output to the attenuator it also brings $R_{23}$ into circuit to reduce the sweep and by $S_{4}$ and $S_{5}$ it reverses the phase of the $50-\mathrm{Hz}$ voltage applied to $\operatorname{Tr}_{3}$.

This is the condition for aligning an inter carrier sound channel. The marker oscillator is set at 39.5 MHz to simulate the vision carrier, and the wobbly oscillator is set by the mid-band frequency controls to sweep about a centre frequency of 33.5 MHz . The $6-\mathrm{MHz}$ beat between the two is developed in the receiver under test just as it is when a television signal is being received.

Reversal of the phase of the $50-\mathrm{Hz}$ drive to $\mathrm{Tr}_{3}$ is by no means essential, but is desirable in order that the frequency sweep shall be in the same direction for both channels. It is desirable to have frequency increasing to the right on the display and the connections are made to provide this


Sequences of traces with the markers moved by 2 MHz in each photo. The slight variation of trace length is caused by mains voltage fuctuation.
for the vision channel. Because the sound channel signal is generated as a difference frequency with the fixed frequency higher than the variable, the same connections would give a sound-channel display with frequency increasing to the left. This is remedied by reversing the phase of one $50-\mathrm{Hz}$ channel.

We now come to the buffer and marker mixer, which is operative only for visionchannel alignment. $L_{3}$ is connected through a potential divider $R_{48}, R_{49}$ to the input of $T r_{5}$. This is a normal r.f. amplifier stage with a tuned collector circuit comprising $L_{4}, C_{19}$ damped by $R_{53}$. It is tuned to mid-band and has a 3 dB bandwidth of 12 MHz . Marker inputs from the internal marker oscillator and from a signal generator are coupled into $L_{4}$ and there mixed with the signal from the wobbly oscillator. The whole is applied to the diode detector $D_{4}$ and the beats between the signals are produced at its output. The marker amplitude control $R_{56}$ is fed through quite a small capacitor $C_{22}$. This has been found desirable to remove some residual hum which otherwise produced a slight unwanted vertical deflection on the c.r.t. The output from $R_{56}$ is mixed with the output of the receiver under test, which necessitates bringing this into the wobbulator instead of taking it directly to the c.r.o.

This output is brought in at the socket "Input from i.f. amp" and is taken through $R_{57}$ of $6.8 \mathrm{k} \Omega$ to the socket marked "Output to c.r.o. Y-amp" and the marker signal is also fed to this through $C_{24}$.

The maximum amplitude of the marker signals is fixed by the design and can only be reduced by $R_{56}$. The amplitude required depends on the peak-to-peak amplitude of the output of the i.f. amplifier. The maximum marker amplitude has been made about right for an i.f. output of about 2 V p -p, and it is usable, although a little small, for outputs up to some 4V. Naturally, for small outputs of under 1 V it is too great, and that is why the amplitude control is provided.

The newcomer to a wobbulator will undoubtedly think the amplitude available is too small, but he will soon find that it is adequate. It is essential that the marker amplitude should not be too great, since if it is it can greatly distort the trace.

The wobbulator is designed for use with an oscilloscope which has provision for an external X-deflection voltage and has some kind of amplitude adjustment for it. It must also have a Y-amplifier which is capable of giving undistorted reproduction of pulses of some 5 ms duration which are repetitive at 100 Hz , for that is what the output signal from the amplifier under test approximates to. An amplifier with a 3 dB response at $50-\mathrm{Hz}$ would be useless. the gain should be such that an input of 1 V p-p will give full Y-deflection, and there must be adequate gain control.

The power supply is shown in Fig. 2 and is self-explanatory. The two $7-\mathrm{V}$ windings of $T_{2}$ could quite well be on the core of $T_{1}$, but this would have necessitated a specially-wound transformer. By using separate transformers two standard components could be employed.

Half-wave rectification is used for both supplies with the diodes $D_{5}$ and $D_{6}$.

## News of the Month

## Television camera design for constructors

The latest and most ambitious design to be issued by the Mullard Educational Service is for a closed-circuit television camera using a 1 -inch vidicon pick-up tube. According to the designers it can be built for about $£ 45$, which is less than half the price of the cheapest professional camera. A model we saw made up and working produced pictures which. although not of professional c.c.t.v. quality, were certainly good and would be acceptable to most schools. technical colleges and individual constructors.

Cost is saved by using a sub-specification vidicon of one of the simpler types (e.g. Mullard XQ1030. Philips 55850 ). by winding your own deflection and focus coils. by circuitry designed for cheap and readily available transistors (e.g. BCY70), by the use of a photographic camera lens rather than a television camera lens, and by an elementary type of housing (e.g. a piece of plastic drain pipe and a tobacco tin lid). In addition the camera circuitry is simplified by the adoption of sequential (non-interlaced) scanning: the model we saw demonstrated was working on $312 \frac{1}{2}$ lines per field, 50 fields per second.

The electronic circuits in the camera
are: a video amplifier with a bandwidth of 4.5 MHz and an output signal of $1 \mathrm{~V} \mathrm{p-p}$ into $75 \Omega$ : horizontal and vertical timebase generators; a synchronization mixer (feeding sync signals into the video amplifier); a blanking mixer (providing blanking pulses at the vidicon cathode): and a power unit ( -15 V for the transistor circuitry and -120 V and +330 V for the vidicon). The circuitry uses 23 transistors of six well-known types and 10 diodes of five types. Several monitors can be operated from the one camera.

To build the camera for $£ 45$ the designers admit that the constructor will have to "shop around" to some extent. but for those who are willing to pay for more to save this trouble, a complete kit of parts is available from Linstead Electronics, Roslyn Works, Roslyn Road, London N. 15 , at $£ 70$ (or $£ 45$ without the tube and lens). This company will also supply individual parts from the kit, and are offering a ready built camera with a professional looking chassis and case for $£ 99$ 17s 6d. The Mullard Educational Service (Mullard House. Torrington Place. London W.C.1), of course. only supplies the design information. Their literature is not yet ready but will be available later.

## R.S.G.B. Exhibition

The Radio Society of Great Britain's International Radio, Engineering and Communications Exhibition will be held at the Royal Horticultural New Hall, Westminster. London S.W.I. from the 19th to 22 nd of August. The exhibition will be open during this period from 10.00 to 21.00 and the admission charge is 4 s .

At 14.30 on the second and third days there will be lectures on mobile equipment and s.s.b. receivers.

Wireless World will have a stand at the exhibition (No. 11) and we plan to demonstrate the phase-locked loop stereo decoder and the television wobbulator described in this issue. We also hope to demonstrate the surface temperature thermometer described in April 1969, the logic display aid described in the May to December 1969 issues and the electronic dice which was described in the April 1970 issue. Also on the stand we shall be selling a selection of books and reprints of some of the articles which have appeared in Wireless World.

Other exhibitors include: Adcola, Amateur Radio Shop, Angus McKenzie Hi-fi. Baginton Electronics, British Amateur Radio Teleprinter Group, British Amateur Television Club, City and Guilds of London Institute, E.M.S.A.C., J. Michael Gale, Garex Electronics, J. Beam Engineering Ltd, K. W. Electronics Ltd, Lowe Electronics, Microwave Modules Ltd, Ministry of Posts \& Telecommunications, Nombrex (1969) Ltd, Practical Wireless, Professional \& Academic Book Exhibition, Radio Amateur Invalid and Bedfast Club, Radio Shack Ltd, Radio and Space Research, R.A.F., Royal Navy A.R.S., Royal Signals A.R.S., Telecomms, Weller Electric Ltd, Western Electronics, World Association of Methodist Radio Amateurs and Clubs.

## CAT-70

The British Amateur Television Club celebrated its 21 st anniversary during the weekend 25 th-26th July with a Conference on Amateur Television ("CAT-70") held at Churchill College, Cambridge.

Over 100 people registered, including delegates from Belgium, France, Germany, Switzerland and the U.S.A.

The major event of the weekend took place on the Saturday afternoon. Signals from several amateur television stations were received and displayed on monitors in the Wolfson Hall. from 14.30 until 16.00. Stations contributing included G6ADM/T from Haddenham, Cambs. ( 11 miles); G6NOX/T from Duddenhoe End, Essex ( 14 miles); G6REH/T from the top of his 110 ft tower at Sutton St. James, Lincs. ( 36 miles); G6AEV/T/A from a caravan in Cambridge ( 2 miles); and G6WI/T in Great Canfield, Essex, relayed via

G6NOX / T giving a total path length of 27 miles. A wide range of equipment was shown by amateurs, ranging from vidicon cameras to integrated circuit colour pattern generators.

The main social event was the Convention Dinner, attended by over 80 people on the Saturday evening.

On the Sunday morning, lectures were presented by C. Grant Dixon on "Slow Scan Television", by Arthur Critchley on "Integrated Circuits for the Amateur", and by M. P. Davies, of the Ministry of Posts \& Telecommunications, on "The Amateur Licence".

## Starting your own business

A conference to be held at Fulmer Grange, near Stoke Poges, from the 27th to 29th of November will appeal to all those with ideas and a hankering to start their own business. For this type of person, with the determination to make a go of it, the conference should be a weekend well spent.

Ten successful entrepreneurs will talk about their experiences, the difficulties they faced and how they overcame them. Other speakers will explain how to raise the necessary finance and how to assess the market. For a period the conference will break up into discussion groups and each one will deal with a particular new business. Finally the type of person most likely to succeed will be discussed.

The fee for the conference is $£ 6$ for a single man but the organizers realize that once the plunge is taken your wife is going to have to share your affections with the business and they feel that she should be in at the start. So for an extra $£ 2$ you can take her along as well! Application forms are available from The Meetings Officer, The Institute of Physics and the Physical Society, 47 Belgrave Square, London S.W.I.

## Hong Kong radio sales halved in Britain

In contrast to the trend in the rest of the world sales of radio receivers manufactured in Hong Kong have fallen in this country from 34 to $17 \%$ of the total market. This means that Hong Kong has slipped to second position behind Japan as far as total U.K. sales is concerned. Hong Kong attributes this decline to their concentration on the six-transistor single waveband receiver for the American market which is not popular here.

These figures are taken from a survey conducted by the Hong Kong Development Council which says that the concentration on the American market results from the heavy U.S. investment in the industry. Eight American firms employ more than a third of Hong Kong's radio
industry's 18,000 work force. Britain's only representative in the industry is Pye who has a $51 \%$ interest in Coronet Industries Ltd, a firm in Kowloon which employs about 600 workers.

## V'enus-Mercury spacecraft

The National Aeronautics and Space Administration have selected seven scientific investigations for the Mariner-Venus-Mercury 1973 (MVM-73) spacecraft to photograph the two planets. measure the particles and fields surrounding them and study their atmospheres and ionospheres. The 900 -pound spacecraft is planned to be launched in the autumn of 1973 and should pass within 3,300 miles of Venus in February 1974 and 625 miles of Mercury in March 1974.

Teams of scientists have been formed to conduct the seven investigations listed below.
Imaging science: Weighing 61 pounds the experiment will employ two television cameras fitted with $1,500-\mathrm{mm}$ Cassegrain telescopes. These will produce pictures of Mercury with a resolution similar to that of pictures of the Moon taken through Earth-based telescopes.

Because three 210 -foot diameter aerials will be in operation in 1974 (two are now under construction at Tidbinbilla, Australia, and near Madrid, Spain), many of the pictures will be transmitted directly to Earth instead of being recorded for later transmission. Some 5,700 frames of Venus and about 2,740 frames of Mercury will be taken.
Radio science: Using radio signals from MVM-73's two transmitters (20-W S-band and $200-\mathrm{mV}$ X-band) the spacecraft's trajectory will provide dual occultation of the radio signals at Mercury and a single occultation of the radio signals at Mercury and a single occultation at Venus. This will provide the investigators with information on the interplanetary phenomena during flight and. at planetary encounters, information on the atmospheres ionospheres, mass, radius and surface characteristics of both planets.
Plasma science: Will use an instrument called a scanning electronic analyser which is a set of hemispherical analyser plates and an electron multiplier mounted on a scan platform. It will measure ions from 80 to $8,000 \mathrm{eV}$ and electrons from 40 to 400 eV . During the flight, the instrument will study the structure of the solar wind between the orbits of Earth and Mercury while the Pioneer-F and -G spacecraft, to be in flight during the same period, will be measuring the solar wind between the orbits of Earth and Jupiter. This will make possible a unique comparison of measurements at wide distances across the solar systems for the first time.
Magnetometer: An experiment to measure the magnetic field, it weighs 11 pounds and uses two triaxial, fluxgate
magnetometers mounted at different distances from the spacecraft on one boom. The magnetometer team will use measurements near Venus and Mercury to make the first experimental study of the solar wind interaction with Mercury and to determine whether or not a magnetic field exists at the planet.
Ultraviolet spectrometer: Consisting of two ultraviolet grating spectrometers, direct studies of airglow and occultation techniques will be used to gather data. The spectrometer team will use the data obtained by solar occultation to search for the presence of an atmosphere on Mercury and to determine its structure and composition. Additional information on the character of the atmosphere of Venus will also be obtained.
Infrared radiometer: Consists of two one-inch-diameter telescopes each calibrated for a broad spectral band to measure temperature emissions from the two planets.
Charged particles: A six-pound instrument will measure electrons above 2 keV and protons above 6 keV .

## 3D colour TV

An experimental broadcast is to be made in Holland on November 9th using a principal which was applied long before the war in cinemas. The viewers will wear spectacles with one red and one green eyepiece so that they will see the programme in three dimensions and in colour.

## Professional engineers', the choice

Members of the fourteen institutions which constitute the Council of Engineering Institutions can opt to join two other organizations which will handle such matters as welfare, pay, conditions and the like. An institution, being a learned society with the object of furthering science, cannot concern itself with the affairs of private individuals.

The engineer who wishes to have the full backing of a trade union, with all that this implies, can join the United Kingdom Association of Professional Engineers (UKAPE). This organization is intent on building a reputation for ethical and responsible conduct but it will also use its powers to protect the individual from exploitation. It aims to improve his conditions of employment and to regulate the relations between employer and employee.

Some engineers may not wish to join a trade union, maybe because they are 'employers themselves or for some other reason, but they would still like to belong to an organization with their welfare at
heart. Such an organization is the newly formed Professional Engineers Association Ltd (PEAL). Members of the institutions within C.E.I. are being invited to join this organization and providing 15,000 do so PEAL say that they will be able to provide an efficient service. If PEAL is successfully launched the assets of the Engineers Guild, which was formed in 1938, will be made available to PEAL.

## Tubes of Babel

If the current demand continues the number of public telephone circuits on Britain's trunk system will double in the next four years. In order to cope with this increase the Post Office have developed a $60-\mathrm{MHz}$ cable which will provide 97,200 circuits. The first example of this cable will be laid in 1973 between London and Birmingham and will be followed shortly after by a similar cable in the reverse direction.

The cable will consist of nine coaxial pairs, or tubes, operating from 4 to 60 MHz . Each pair will carry twelve 900 -circuit broadbands using a frequency division multiplex system. Repeaters, energized over the cable from power feeding stations, will be placed every 1,500 metres to compensate for the high attenuation in the cable at 60 MHz . The cable will be laid in a specially constructed concrete duct deeper than is normal for telephone cables and access will be through manholes.

## C.E.I. changes its exam

Part 1 Of the Council of Engineering Institutions' examination-describable as "what every engineer should know"-has not so far been very successful in the radio-electronics sphere in the sense that few aspiring engineers have chosen to take it and even fewer have passed. To make it more attractive the C.E.I. has made some changes, both in subject matter and standard, which will come into force in 1972.

Originally Part 1 consisted of six compulsory subjects, of which only one, applied electricity, had to do with electro-technology, and the standard was equivalent to about half way through a three-year degree course. At present the electronics man can, if he wishes, replace three of the six (properties of materials, applied thermodynamics, fluid mechanics) with three subjects more closely related to electronics. The changes for 1972 will be the introduction of certain optional subjects and a reduction of the standard to a point about 12 months through a three-year degree course. Passes will be required in four compulsory subjects, mathematics, mechanics, properties of materials, and presentation of engineering information, and in two of the following
optional subjects: electrotechnics, electronics, chemistry, thermodynamics.

Details of the changes, syllabuses and specimen papers are given in C.E.I. Statement No. 8 which may be obtained from the C.E.I. (2 Little Smith Street, London S.W.1) or any of its constituent institutions, price 4 s od post free. Also under review is Part 2 of the exam, but any changes which may result will not come into effect until 1974 at the earliest.

## Colour receiver sales

During June 38,000 colour television receivers were delivered to the trade. This is 2,000 more than in May and brings the total number of deliveries since the inauguration of the colour service in 1967 to half a million. The upward trend is illustrated by the fact that half of this total ( 0.25 M receivers) have been delivered during the last nine months. The increasing sales of colour receivers is reflected in a slight slackening in sales of monochrome sets [1970 (1969), May 133,000 (149,000). June 124,000 $(135,000)$ ). Single standard monochrome receivers accounted for $40 \%$ of the June total.

## Experimental communications link

A 30 km experimental communications link which uses a 50 mm circular waveguide to transmit up to 300,000 simultaneous two-way telephone conversations or 200 colour television channels is to be installed by the Post Office between the research station at Martlesham Heath and Mendlesham in Suffolk. The Marconi Company Research Division is to develop and supply the prototype terminal and repeater equipment under a Post Office contract worth $£ 180,000$.

For the experimental link the frequency range will be divided into two main bands, 32 to 50 GHz and 50 to 90 GHz , although ultimately, this will be extended to 100 GHz .

## Correction

Phease make the following amendments to Fig. 9 of the article "Electronic Morse Keyer" by C. I. B. Trusson and M. R. Gleason published last month. On the upper view of the circuit board the lead from the tune/operate switch should be connected to pin 3 of the MP 104 (not pin 2) and the pin numbering of the MP 102 should be altered to read 5 to 9 from top to bottom on the left-hand side and 4, 3,2, 1, if on the right-hand side. On the underside view of the board the pin numbering of the MP102 should be amended as described and the position of the conductor breaks at the following points should be lowered by one position: 29/22, 29/28, $25 / 22,26 / 33,28 / 37,27 / 37$. Finally the break at $11 / 41$ should be moved one place to the right.

## H.F. PredictionsSeptember

Seasonal change is evident as a slight increase in peak median standard usable frequencies (MUFs). This is sustained during daylight on all routes illustrated except Hong Kong which, due to the large time difference between control points, develops a continuously varying MUF.
MUFs shown are predicted medians of day-to-day values for the month. Distribution of daily values about the median varies with geographic location, season and time of day. Long-term observations have shown that the optimum traffic frequency (FOT)-i.e. MUF exceeded on $90 \%$ of days-is between $72 \%$ and $90 \%$ of MUF. A constant $85 \%$ is used for these charts, prepared by Cable \& Wireless.





# The programmable unijunction 

by O. Greiter

The unijunction transistor and some of its applications have been described in articles in Wireless World, last month and the month before. To remind readers who have never met the unijunction we may note that it consists essentially of a silicon bar with an ohmic, non-rectifying, contact at each end and a tapping point near the middle. It is a resistor with a tap, except that the tap is a rectifying junction: one junction, hence the name. With a voltage applied to the bar it behaves just as a fixed-tap potentiometer with a diode in series with the tap. Unless the bias on the diode exceeds the sum of the diode starting voltage and the voltage at the tap, the diode is cut off. The tap is about two-thirds of the way along the bar, and this fraction is called the stand-off ratio. Problem: how accurately can you attach a tap to a sliver of silicon? The geometry actually used makes the problem even more difficult, so that the production line standoff ratio has a wide tolerance and it costs extra money to get even a moderate tolerance.
When the diode is brought into conduction carriers are injected into the silicon bar, and as they are swept into the bottom part of the potentiometer they alter its resistance, drop the tap ratio, let more carriers in through the diode and so on. Rather like a one-man band, each part of the unijunction plays many parts.
The disadvantage of this device is that the tolerances must be dealt with in the external circuit. Oscillators and timers need to have a wide range of adjustment to take up the tolerance in the stand-off ratio, and this is particularly objectionable if it is required to choose components with the right temperature coefficients to compensate for the temperature changes in the unijunction itself.

## The PUT

The programmable unijunction, so-called because the parameters are fixed by external elements and because it has three junctions, not one, gets rid of many of the disadvantages of the standard unijunction, even though it is just about the same price. It is officially described as a complementary thyristor, although by thyristor standards it is a very low level device indeed. We shall see that it is related to another, older, device.


Fig. 1. The structure and symbol for a programmable unijunction transistor, showing anode, gate (anode gate) and cathode connections.



Fig. 2. Adding resistors $R_{1}$ and $R_{2}$ to the PUT, gives the equivalent of the ordinary unijunction.

The basic structure of the PUT and the symbol used are shown in Fig. 1. In normal use the basic connection, the starting point, is to set up the simple circuit of Fig. 2. The gate is connected to the junction of $R_{1}$ and $R_{2}$, so that the upper junction is held at $\eta V_{s}$
where $\eta=R_{1} /\left(R_{1}+R_{2}\right)$. This is just what we have in the unijunction, except that now $R_{1}$ and $R_{2}$ are ordinary resistors, which we can choose of any value, and any tolerance, we like. We can fix the stand-off ratio with as much precision as our money will buy, and certainly $1 \%$ will not cost very much.

So far we have added two resistors, and the cost of connecting them. However, in an ordinary unijunction circuit we put a resistor in the B2 lead, both to limit the current and, by choosing the right value for a particular specimen, to get the right temperature coefficient. We also need, in mañy circuits, a resistor in the B1 lead so that the current through the untriggered B2-B1 path will not flow through the thyristor gate, or transistor base, which is to be pulsed. In the quiescent state there is no current out at the cathode of the PUT and unless a resistor is needed for other reasons, to help with the voltage rating of the load device, for example, we need not use one. Thyristor trigger circuits thus come out, as we see in Fig. 3, with exactly the same number of components.

## Performance analysis

The standard description of the behaviour of thyristors is based on the operation of cutting the device diagonally. This (shown in Fig. 4) allows the three junction device to be split into two transistors, forming an interconnected $p-n-p, n-p-n$, pair. The equations are

$$
\begin{aligned}
& I_{c 1}=h_{f e 1}\left(I_{c 2}\right)+\left(h_{f e 1}+1\right) I_{c o 1} \\
& I_{c 2}=h_{f e 2} I_{c 1}+\left(h_{f e 2}+1\right) I_{c o 2}
\end{aligned}
$$

The input current at the anode is

$$
I_{A}=I_{c 1}+I_{c 2}
$$

Solving these equations gives

$$
I_{A}=\frac{\left(1+h_{f e 1}\right)\left(1+h_{f e 2}\right)\left(I_{c o 1}+I_{c o 2}\right)}{\left(1-h_{f e 1} \cdot h_{f e 2}\right)}
$$

At very low currents, $h_{f e 1}$ and $h_{f e 2}$ are very small and $I_{A} \bumpeq I_{c o 1}+I_{c o 2}$. Thus if the currents are small, the gain is low and thus the currents are small. As soon as we apply forward bias to either base we raise the value of $h_{f e}$ for that transistor and in consequence let more current flow into the other; raising its $h_{f e}$, thus, and so on. When the

Fig. 3. In a practical scheme the number of components is the same
 with unijunction and PUT.

Fig. 4. The classic thyristor analysis.

product $h_{f e 1} \cdot h_{f e 2}$ reaches unity, $I_{A} \approx \infty$.
A more elegant analysis can be carried out using the circuit of Fig. 5. If we use the current gain, emitter to collector, notation,


Fig. 5. Resistors added for more detailed analysis.
the overall current gain, $I_{\text {out }} / I_{\text {in }}=\alpha$, is given approximately by

$$
\alpha=\frac{\alpha_{1} R_{2}}{\left(1-\alpha_{2}\right) R_{2}+R_{3}}
$$

and the input impedance at $P$ is

$$
R_{i n}=\kappa-R_{1}\left[\alpha \alpha_{2}-\left(1-\alpha_{1}\right)\right] .
$$

Here $\kappa$ is a positive term which contains device impedances. Very simply this boils down to a condition that the input resistance is negative if $R_{1}\left[\alpha \alpha_{2}+\alpha_{1}-1\right]>r_{e 1}$, the base-emitter input resistance of the p-n-p device.

The addition of these resistance elements, and the inclusion in a full analysis of the device resistances, leads to a situation in which the negative region of $R_{\text {in }}$ has a reasonably constant value. The infinities do not appear. The overall characteristic becomes something like the one shown in


Fig. 6. This, with its peak point and valley point, where both transistors are bot tomed, is just the shape we have already seen for the unijunction. Some of us, indeed, have already seen this a good many years ago. Fig. 7 shows a common base amplifier, without the supply connections. The input impedance at the emitter is

$$
R_{i n}=r_{e}+(1-\alpha) R_{B} .
$$

A negative resistance will be obtained if

$$
(\alpha-1) R_{B}>r_{e}
$$



Fig. 7. In this circuit $R_{B}$ includes the internal $r_{b}$.

$$
\alpha>\left(r_{e}+R_{B}\right) / R_{B}
$$

## The PUT as a point-contact transistor

Those readers who cut their teeth on junction transistors will regard this as a rather pointless exercise. Those who spent confused years with point-contact transistors will know that $\alpha$ can be greater than unity, and will remember that a stable amplifier needed a low impedance in the base line. The point contact transistor was, in general, a p-n-p-n device, but this was not an essential piece of knowledge. The essential detail was that you could measure $\alpha$ and it was greater than unity.

By accepting the fact that, current ratings apart, the PUT can be considered as a point contact transistor, we are free to look at various pulse circuits which we used twenty years ago. We can also get rather more "feel" to the conventional use of the PUT. The circuits of Fig. 2 can be rearranged in


Fig. 8. The basic gate supply circuit, for PUT, and base bias for point-contact transistor.
the form of Fig. 8. We see that $R_{B}$ is, in fact, the parallel combination, $R_{1} R_{2} /\left(R_{1}+R_{2}\right)$. The peak point, at which $R_{\text {in }}=0$, will be when

$$
\alpha-1=\frac{r_{e}}{R_{B}}
$$

Memory, always a bad guide, suggests that $\alpha$ was not very dependent on current at low levels. The current dependent term is $r_{e}$. This would give us a peak point which was dependent in just the same way on $R_{B}$ and we would expect to be able to choose the peak point current by choice of $R_{B}$. It turns out that this is indeed so, and the curves for a cheap and a more expensive


Fig.9.From G.E. data. $I_{p}-V_{5} \cdot R_{G}$ parameter.


Fig. 10. From G.E. data. $I_{v}-V_{5} \cdot R_{G}$ parameter.
type of PUT shown in Fig. 9 shows this quite clearly. For high values of $R_{G}=R_{B}$, the peak point current is very small.

It is not surprising that the valley point current is also very dependent on the gate supply impedance. The characteristics are shown in Fig. 10. Very roughly we see that $I_{v}=100 I_{p}$. It is a feature of the PUT, however, that these characteristics are determined by an external element. An approximate expression for the impedance looking in at the base is $Z_{B}=r_{b}+\left(\frac{1}{1-\alpha}\right) R_{E}$.

Forgetting the internal $r_{b}$, and looking for the turning point at which $R_{B}+Z_{B}=0$

$$
(\alpha-1) R_{B}=R_{E}
$$

We can get results rather nicely if $R_{B}$ is very large indeed, and since the peak point current is small the base current will be small. A non-linear resistance element will give just the right effect of high resistance round the peak point but, when the current increases, a low resistance to allow a high valley current to be set up. Two ways of
(a)

(b)


Fig. 11. Two ways of getting a low value of $I_{p}$ combined with high $I_{v}$.
connecting this are shown in Fig. 11. The off-state gate current is very small, less than $0.1 \mu \mathrm{~A}$, so that it is desirable to stabilize the peak point working condition by means of a $1 \mathrm{M} \Omega$ resistance. This is the form shown in Fig. 11(a). In Fig. 11(b) the gate supply impedance is not so high, as the arrangement leads to a small drain current down
through the diode and $1 \mathrm{M} \Omega$. The equivalent gate supply impedance is then between five hundred thousand and seven hundred thousand ohms. However, if the diode is reasonably similar to the upper p-n junction of the PUT and is operated at a current equal to the peak points current-say 1.5 A for the D13TI-the two temperature coefficients will stay in balance and the device will always trigger at $V_{A}=V_{o}$.

Both these circuits give a ratio $I_{v} / I_{p}$ of above 500 , compared with the ratio of about 100 if the diode is not used. It is probably desirable to look at the detail of this diode temperature compensation in terms of the point contact transistor. In Fig. 12 the transistor is shown with a leakage resistance $R_{t}$ from base to collector. This represents the current path at the peak point. The circuit reduces then to the bridge form on the right, in which the "detector zero" is


Fig. 12. Temperature compensation in terms of the point-contact transistor, and the bridge equivalent.
obviously maintained so long as the two diodes stay in step. One might expect that without going to an individually matched solution the improvement would be a factor of about 10 . Just what the original temperature dependence would be is a matter of the form of the circuit. The data sheets give temperature curves, but they do not line up with the other characteristics. Nor do the characteristics shown in Figs. 9 and 10 line up with the tables. The data sheet information is added as an appendix.

## Operational limits

Once we know what a device will do, in the sense of knowing that nature of its performance, we need to know the quantity of its performance, and the sort of circuit in which that performance can be exploited. The PUT is limited to 40 V working and to a steady state current of 150 mA -say 100 mA for a reasonable temperature range. It is imprudent to ask for pulses of more than 0.5 A . The maximum discharge, in an $R C$ oscillator, with no extra resistance to limit the current, is $250 \mu \mathrm{~J}$. This means that if the circuit uses a $4 \mu \mathrm{~F}$ capacitor you should see that it triggers at below 10 V , so that $\left(\frac{1}{2}\right) C V^{2}=\left(\frac{1}{2}\right) \cdot 4 \cdot 10^{-6} \cdot 10^{2}=200 \mu \mathrm{~J}$. In such a circuit, the supply resistance will probably need to be more than $50 \mathrm{k} \Omega$ and less than $10 \mathrm{M} \Omega$ with the cheap device. The time range thus extends up to about half a minute.

## Relaxation oscillator

The most common circuit application is in the simple relaxation oscillator shown triggering a thyristor in Fig. 3. The capaci-


Fig. 13. Relaxation oscillator behaviour.
tance $C_{T}$ is charged through $R_{T}$ until the peak point is reached. The PUT is triggered, to discharge $C_{T}$ into the cathode load. As this is much the same as the unijunction we can use Fig. 13 to remind us that the anode voltage moves up on the first stroke from zero towards B , along the path AB . At B the voltage can no longer be sustained across the PUT, and since the voltage across the capacitor will not change instantaneously the system switches to the only stable point, out beyond C. During the flight, current is flowing, and the voltage drops to give an intersection in the region $C$. The only current which can be supplied through $R_{T}$ is much less than this, and the capacitor discharges, carrying the working point down to $D$. For the working point to approach $I_{o}$ it would be necessary to follow the path $\mathrm{D} I_{o} . C_{T}$ is not capable of changing its voltage quickly upwards, because it can only charge through $R_{T}$. The working point jumps from $D$ to $A$. There are some much more elegant ways of treating this circuit. We could use the negative resistance concept and look for the way the root dodges about between the left-hand side of the plane and the right-hand side. No doubt some of the brighter contributors to Wireless World will explain all this to us one day. The simple approach tells us how it behaves, if it works: the theory tells us if it works.

Notice that the $R_{T}$ load line must cut the device characteristic once only, in the negative impedance region. This means, very roughly

$$
\frac{\eta V_{s}}{I_{p}}>R_{T}>\frac{V_{s}}{I_{v}}
$$

To get a particular frequency we choose $R_{T}$ within this range, and then put

$$
\begin{aligned}
C_{T} & =\frac{1}{f R_{T} \log \left(\frac{1}{1-\eta}\right)} \\
& =\frac{1}{f R_{T} \log \left(1+R_{1} / R_{2}\right)}
\end{aligned}
$$

If we make $R_{1} / R_{2}=1.7$ this reduces, since $\left.\log e^{( }\right)=1$, to a simple equation: $f C_{T} R_{T}=1$.

A disadvantage of the PUT is that in general the value of $R_{T}$ needed for operation is a good deal higher than the value used in the corresponding unijunction circuit. Fortunately the fact that it is operating by transistor action rather than by resistance modulation means that it comes on quick and it comes on hard. The saturation voltage at 50 mA is 1.5 V , giving a saturation resistance of $30 \Omega$ maximum, and they say
that this drops to $3 \Omega$ at higher currents. The switching time is fast, $60-80 \mathrm{~ns}$. A quick calculation shows that if we take 100 mA from a 1000 pF capacitor it will discharge at the rate of 7 V in 70 ns . Thus we shall not swing down to an unreasonable trajectory until we go below the $0.001 \mu \mathrm{~F}$ value of $C_{T}$. Rather roughly, we lose half our pulse. With the ordinary unijunction the limit is in the region of three times this value.

## Other PUT applications

There is a useful G.E. application report ( $90 \cdot 70: 11 / 67$ ). Some of the following circuits are taken from this report, which also contains some thyristor trigger circuits. The first is a particular relaxation oscillator, which operates at only 3 V . The circuit is shown in Fig. 14. In this low voltage circuit


Fig. 14. 1 kHz oscillator for 2 V working.
there is the problem that the voltage needed to get the first junction into conduction, the emitter-base voltage of the equivalent point contact transistor, is an important fraction of 3 V . The anode gate is held at about 1.2 V , so that the anode must be brought up to about $1 \cdot 7-2.0 \mathrm{~V}$ for triggering. If the more conventional stand off ratio of around $\frac{2}{3}$ had been used, the capacitance would have had to charge to above 2.5 V on its exponential run up to 3 V . This would mean a very flat approach to triggering and a great deal of uncertainty about the frequency, stroke by stroke. This circuit also gives very low drain on the battery. The total current is less than $100 \mu \mathrm{~A}$. A conventional low voltage unijunction would demand about 1 mA .

Circuit action in which advantage is taken of the low operating current levels is exemplified by the circuit of Fig. 15. The


Fig. 15. Tone-pulse oscillator.
zener diode-diode circuit can be replaced by the emitter-collector path of a small transistor. As it stands, the $100 \mu \mathrm{~A}$ available at the anode through the $100 \mathrm{k} \Omega$ resistance will hold the PUT, a low-current type, beyond the valley point. If the switch is
closed for a short time the $10 \mu \mathrm{~F}$ capacitor is charged, biasing the diode off and leaving only the $1.8 \mathrm{M} \Omega$ resistor to supply the anode. This is an oscillatory situation, and the circuit runs at about 1000 Hz until the capacitor has discharged through the $100 \mathrm{k} \Omega$ to the point where the zener diode will conduct. With the values shown the tone should be on for about 1 second.

Timers. These are basically oscillators of which the frequency is so low that all the attention is concentrated on a single cycle. The important advantage of the PUT is that because the stand-off ratio is determined by two external resistances almost all the parameters of the timer can be selected in advance. The circuit shown in Fig. 16 uses


Fig. 16. 30-second timer using expensive PUT.
$1 \%$ tolerance components. The stand-off ratio is $0 \cdot 61$, or $R_{1} / R_{2}=1 \cdot 69$, which agrees with our earlier finding that this is the value to make $f C_{T} R_{T}=1$, or

$$
\tau=C_{T} R_{T}
$$

The effective value of $R_{G}$ is not too certain, but the circuit does not make sense if it is above $1 \mathrm{M} \Omega$ : it is the resistance of the diode when passing about $1.5 \mu \mathrm{~A}$. The peak-point current will be in the region of $0.1 \mu \mathrm{~A}$. This can be supplied by the $30 \mathrm{M} \Omega$ resistor. It would appear that trouble might occur at very low temperatures. At $-25^{\circ} \mathrm{C}$ the peak point current is $1 \mu \mathrm{~A}$, and there is only $0.3 \mu \mathrm{~A}$ available. The circuit could stick just below peak point.
To operate a circuit of this kind at low temperatures, or to use the cheaper PUT, the technique is to pulse the anode gate. This technique was described in connection with the conventional unijunction. The


Fig. 17. Modified circuit of $30-\mathrm{sec}$ timer to use cheaper PUT.
modified circuit is shown as Fig. 17. The application report quotes a $10 \mu \mathrm{~s}$ pulse at 1000 Hz , but as the circuit is a 30 -second timer in the $1 \%$ class it would be reasonable to settle for a much slower sampling rate.
Time or frequency trimming is claimed to be much simpler with the PUT. The comparison made is with trimming provided


Fig. 18. Two alternative ways of frequency trimming.
by means of a variable resistance in $R_{T}$ itself. It is, however, possible to trim the frequency of the unijunction and PUT circuits in the timing path in a way which still leaves a lot of flexibility in the choice of values. The two alternative ways of adjusting the frequency over a small range are shown in Fig. 18.

A number of other applications are to be found in the GE application report, which is essentially thyristor-minded in the view of this writer. The circuits for ring counters and thyristor triggering are interesting and useful, but there are some speculations to which the remaining space in this article may well be devoted.

We have seen that the PUT is very much like a point contact transistor. One difference, of course, is that it is a silicon device, whereas all, or at any rate almost all, the point contact transistors were germanium devices. The other feature is that junction technology has given us very low saturation resistance, thus widening the available working band inside the supply voltage. For the D13T1 we find that at $10 \mathrm{~V} V_{s}$ we have a valley current of 1 mA with an $R_{G}=1 \mathrm{k} \Omega$. This valley current gives an average value of

$$
R_{i n}=10 \mathrm{k} \Omega
$$

so that, roughly

$$
(1-\alpha)=R_{i n} / R_{B}=R_{i n} / R_{G}=10
$$

Thus $\alpha=11$

$$
\begin{aligned}
& \text { At } R_{G}=R_{B}=10 \mathrm{k} \Omega \\
& \quad R_{i n, e}=-10 / 0 \cdot 25=-40,000
\end{aligned}
$$

Thus $\alpha=5$.
It is apparent that the equivalent point contact transistor is a rather non-linear device of rather uncertain characteristics. Even so, there is no reason why we should not attempt to use the PUT in some of the circuits which were evolved in the days of the point contact transistor. Fig. 19 shows a greatly simplified equivalent commonbase amplifier. The input impedance of this arrangement has already been given, on the assumption that $R_{c}$ is small. The input impedance of the common emitter circuit


Fig. 19. Common-base point-contact circuit.
is, in simplified form

$$
R_{i n, b}=R_{B}+\left(\frac{1}{1-\alpha}\right) R_{c} .
$$

This gives a negative resistance for the same condition as for the common base circuit. The difference is that with the common base circuit the impedance at the emitter line input is open-circuit stable, while with the common emitter circuit the impedance at the base input is short-circuit stable. We have already seen how, by putting a device which is a short-circuit at very high frequencies across the emitter input we achieve instability which drives the system from one limit condition to the other. This is the capacitance or controlled relaxation oscillator. The same effect can be produced by the use of inductance in the base circuit. A relaxation oscillator can be constructed using the arrangement of Fig. 20. The setting-up condition is, as in the


Fig. 20. Inductance controlled relaxation oscillator.
$R C$ circuit, the choice of $R_{E}$ to give a static current which is between the peak point and the valley point. If the effective value of $R_{B}$ is $10 \mathrm{k} \Omega$ and, to make life simple we take $R_{1}=R_{2}=20 \mathrm{k} \Omega$, and $V_{o}=20 \mathrm{~V}$, the valley current will be rather over $200 \mu \mathrm{~A}$. A good mid-point will be at $I_{o}=100 \mu \mathrm{~A}$, giving $R_{E}=100 \mathrm{k} \Omega$. At very high frequencies the inductance will hold the base current constant, and if instantaneously this base current is insufficient to allow $100 \mu \mathrm{~A}$ to flow the circuit will progressively cut itself off. Base current will disappear, because of the movement of the emitter. There is a voltage spike at the base, just as in the $R C$ circuit there is a current spike when the circuit triggers. The whole action can be described on a negative resistance S-curve. It is not profitable to go into detail, because the actual device has been designed to handle high peak currents, but not to handle high peak voltages.

More interesting, from a practical point of view, are the circuits shown in Fig. 21. These two circuits provide the required high or low impedance required for oscillation at a single finite frequency. These oscillators

are simple but are not likely to be very high class circuits, relying as they must on a very non-linear negative resistance to maintain oscillation, and a sharp limiting action to determine the amplitude. If we continue on the lines suggested by point contact transistor experience we arrive at a circuit of the type shown in Fig. 22, in which a low


Fig. 22. High stability should be obtained by decoupling and a tapped tank circuit.
inductance, high- $Q$, circuit is used together with a good deal of decoupling. It would seem to be reasonable to add a thermistor in parallel with the $L C$ circuit to set the amplitude of oscillation so that it remains inside the cut-off and saturation regions of the transistor.

One area in which the point contact transistor is missed is in the design of simple pulse regenerators. It is thus interesting to compare two circuits, one for a point contact device and one for a PUT (Fig. 23). The PUT circuit produces the output pulse when the transistor is switched off. If we consider the essential circuit as a monostable we see that the only real difference is in the choice of trigger points.


Fig. 23. Two ways of producing standard sharp pulses.

The purpose of this article, and of the two of the conventional unijunction which preceded it, has been to draw the attention of readers who have not met these devices to the wide range of circuits in which they can be applied. The PUT, in particular, would seem to be of much wider application as a transistor than is implicit in its official designation of a general purpose low power thyristor. There is enough circuit information on point contact circuits which may be applicable to keep a lot of people happy for a long time.

Fig. 21. Negative resistance LC oscillators.

## Conferences and Exhibitions

Further details are obtainable from the addresses in parentheses

## LONDON <br> Sept. 7-9

Imperial College
Computational Physics
(I.P.P.S., 47 Belgrave Square, London S.W.1)

Sept. 7-11
Grosvenor House
International Broadcasting Convention
(I.B.C., c/o I.E.E., Savoy Place, London WC2R OBL)
Sept. 15-18
Savoy Place
Gas Discharges
(I.E.E., Savoy Place, London WC2R OBL)

Sept. 15-18 Olympia
Bio-medical Engineering Exhibition
(U.T.P. Exhibitions Ltd, 36-37 Furnival Street, London E.C.4)
Sept. 22
William Beveridge Hall, University of London
Computer Output on Microfilm
(Microfilm Association of Great Britain, 109 Kingsway, London WC2B 6PU)
Sept. 28-Oct. 1
Centralised Control Systems
(I.E.E., Savoy Place, London WC2R OBL)

## BIRMINGHAM

Sept. 18-20
The University
The Nuffield Advanced Physics Course
(I.P.P.S., 47 Belgrave Square, London S.W.1)

BRIGHTON
Sept. 15-17
Hotel Metropole
Power Sources Symposium
(International Power Sources Symposium
Committee, P.O. Box 136, 26 Wellesley Road,
Croydon, CR9 2EG, Surrey)
DURHAM
Sept. 2-9
British Association Meeting
(British Association for the Advancement of Science, 3 Sanctuary Bldgs, 20 Gt. Smith Street, London S.W.1)

## EXETER

Sept. 15-18
The University
Solid State Devices
(I.P.P.S., 47 Belgrave Square, London S.W.I)

## HARROGATE

Sept. 18-20
Cairn Hall
Audio 70
(Exhibition \& Conference Services Ltd,
Victoria House, Claremont Avenue, Harrogate)

## MANCHESTER

Sept. 8-11 Hotel Piccadilly
Electronic Instruments Exhibition
(Industrial Exhibitions, 9 Argyll Street, London WIV 2HA)

## OXFORD

Sept. 14-16
The University
Photo-electron Spectroscopy
(I.P.P.S., 47 Belgrave Square, London S.W.I)

Sept. 28-Oct. 1
New College
Quality Assurance in Action
(Inst. of Engineering Inspection, 616 Grand
Bldgs, Trafalgar Square, London W.C.2)

## READING

Sept. 7-9
The University
Ion Implantation
(I.P.P.S., 47 Belgrave Square, London S.W.1)

SHEFFIELD
Sept. 22-24 The University
Microwave and Laser Instrumentation
(R. A. Ganderton, Design Electronics, Dorset

House, Stamford St., London S.E.I)
SOUTHAMPTON
Sept. 7-10 The University
Measurement Conference
(British Society for Strain Measurement, 281
Heaton Road, Newcastle upon Tyne NE6 5QB)
Sept. 22-24
Skyway Hotel
Electronic Instruments Exhibition
(Industrial Exhibitions, 9 Argyll Street, London WIV 2HA)
SWANSEA
Sept. 21-24 University College
Electronic Engineering in Ocean Technology
(I.E.R.E., 8-9 Bedford Square, London W.C.1)

## TEDDINGTON

Sept. 2-4
National Physical Laboratory
Man-Computer Interaction Conference
(I.E.E. Savoy Place, London WC2R OBL)

WARWICK
Sept. 21-23
The University
Temperature Measurement
(I.P.P.S., 47 Belgrave Square, London S.W.1)

OVERSEAS
Aug. 31-Sept. 4
Munich
Hybrid Computation
(Prof. Dr. J. Heinhold, Kongressburo AICA-
IFIP 1970, Institut fur Angewandte Mathe-
matik, Arcisstr. 21, D-8 Munchen 2)
Sept. 8-12
Magnetic Recording Conference
(Hungarian Optical Acoustical and Fil technical Society, Keszült: 200-pld-ban 70/ 2808-MTESX HNY.Bp.)
Sept. 18-27
Berlin
German Industries Exhibition
(Berliner Ausstellungen, 1 Berlin 19, Charlot-
tenburg, Messedamm 22)
Sept. 21-24 Panama City
Engineering in the Ocean Environment
(I.E.E.E., 345 East 47th Street, New York, N.Y. 10017)

Sept. 23 \& 24
New York
Electron Device Techniques
(I.E.E.E., 345 East 47th Street, New York,
N.Y. 10017)

# Vehicle Location Systems 

# Electronic techniques to improve road traffic control 

by R. A. Tyler*, M.I.E.R.E.

It has been standard practice in the past to apply static means of control to traffic movements, i.e. road signs, markings in the road, fixed 'one-way' systems, etc, but as traffic flow is a dynamic function, adequate control has demanded dynamic methods, such as traffic lights and policemen on point duty. By applying more modern control techniques we should be able to progress a particular vehicle through a traffic system from starting point to destination in the most economical way. Although cost effectiveness at present precludes the use of such techniques for the benefit of the ordinary motorist, the advantages afforded a vehicle fleet operator in being able to control the dispositions of his vehicles in a given area make such a system attractive.

A promising scheme is to provide a supervisory control facility which, by continuous situation reporting, enables route plans to be revised and corrective measures to be reported to the vehicles involved (Fig. 1). Radio links which have voice, data, or voice and data channels can carry the necessary information between vehicle and base, and control room devices exist for displaying this information. However, in order to provide an overall control system there remains the need for a method of determining the position of the vehicle to a sufficiently high degree of accuracy within the traffic system.

The ease with which a vehicle position may be determined depends largely on the vehicle operating mode and the degree of co-operation which may be expected from it. Land transportation vehicles may operate in any of the following three modes:
(a) Free range-where vehicles are allowed to move about without restriction over a specified two-dimensional space, as when operating in a desert environment.
(b) Road restricted-in which vehicles, usually wheeled, are free to move anywhere within the confines of a predetermined road network. This category includes private cars, police and emergency vehicles, etc.
(c) Route plying-vehicles restricted to particular routes within a specified road or rail network. All rail vehicles are included in this group. Although fundamentally of

* The Marconi Company Ltd.


Fig. 1. Vehicle control loop.
type (b) buses may be considered as a sub-group in that they are usually constrained to the route-plying mode.

Clearly, the greater the number of constraints on a vehicle the easier it is to track. A mode (c) vehicle may be quite satisfactorily tracked along the route simply by a knowledge of start time and distance travelled.

Taking full advantage of up-to-date technology it is possible to rule out the use of radio telephone links, which demand a high degree of crew participation, and confine discussion to consideration of location systems which can automatically provide a fixed base station with regularly updated vehicle position information.

Location methods fall into two main categories. The first requires means of discovering the whereabouts of the vehicles directly from the base station. The second needs each vehicle to be provided with equipment to determine its own position and for passing this information to the base station. By using radio, both methods become practicable.

## Location methods, category 1

Radio location systems falling into this category include those employing direction finding, navigation and radar. Direction finding does not easily lend itself to automatic detection of large-vehicle fleets, and ground clutter problems present considerable difficulties when using conventional radar systems.

The most promising approach would appear to come from the use of navigational aid methods which apply triangulation techniques to a signal
radiated from the vehicle. Location accuracies of better than half-a-mile within an area of open terrain of $20-30$ miles radius have been achieved using phase comparison, and there is no reason to suppose that this represents the limits of either range or accuracy. A major difficulty encountered with all methods where location information is to be extracted by reference to the physical nature of the radiated signal is one of multi-path reflection.

Although this difficulty is considerably reduced over areas of open countryside, it remains perhaps the most serious problem in urban environments. Early expectations of using first returned pulse (FRP) delay measurements have been shown experimentally to be disappointing. In this method the vehicle carries a pulsed transmitter which is triggered from the master base station. The difference in delay of the reply pulse from the vehicle arriving at two separated slave receiving stations is related to the receiving station base line, and the vehicle position may then be fixed using standard hyperbolic navigation techniques.

When multi-path propagation conditions exist the vehicle reply appears as a string of pulses at the receiving stations and it is difficult to determine the vehicle position (Fig. 2). In FRP systems, delay comparison is made only on the first pulse to return in each case as this must have arrived over the direct path and later pulses are neglected. Provided that the first pulse to return can be positively identified, this somewhat complex method can be used quite effectively. But in heavily built-up areas the welter of closely spaced reflected signals makes definition of the first returned pulse difficult and the accuracy of such a system thereby suffers. Also the FRP system is in considerable difficulty where more than one vehicle is involved unless selective calling is used. However, this principle may be applied to vehicles operating in any of the three modes referred to previously.

Operation in urban environments, where road junctions frequently occur at less than one hundred-yard intervals, imposes stringent accuracy requirements on any method of vehicle location Accuracies of one hundred feet or less are simply not feasible in such an environment
when using any of the methods in this category. Thus, we have to look elsewhere for a workable solution to the location problem, and from what follows it will be seen that methods falling into the second category show more promise.

## Location methods, category 2

This method is basically the same as the simple one referred to in Category 1, but the vehicle is expected to know where it is at all times. It is, in effect, questioned on its position whenever the base station requires to update its record of vehicle dispositions.

The problem therefore may be split into two requirements, (a) some form of location equipment within the vehicle which allows it to determine its own position, and (b) a means of transferring this positional information back to base on demand.

There are a number of ways of achieving the requirement outlined in (a), two of which will be dealt with in greater detail later. But in order to use this method requirement (b) demands some form of communication channel between vehicle and base and some important experiments in the development of one such link will now be described.

## Data link 1

In the planning stage a number of constraints were placed on the information channel such that the following initial specification was considered desirable.


Fig. 2. Anomalies which can occur in a pulsed system.
$t_{A}$ represents path $A-V$ taken with $t_{B}$ giving vehicle position $V$
$t_{A}^{\prime}$ represents path $A-R-V$ taken with $t_{B}^{\prime}$ giving vehicle position $V^{I}$ $t_{B}$ represents path $B-V$ taken with $t_{4}$ giving vehicle position $V^{I I}$
$t_{B}^{\prime}$ represents path $B-R-V$ taken with $t_{A}$ giving vehicle position $V^{I I I}$
By using the first returned pulse method only delays $t_{A}$ and $t_{B}$ would be used to fix the position of the vehicle at $V$.


Fig. 3. Block diagram of vehicle equipment (top) and base equipment (below).

Printer
(1) The radio part of the link should consist of commercially available two-way v.h.f. equipment, so the information must be fitted into a baseband a few kHz wide.
(2) Selective calling of vehicles was essential for the interrogation methods used. As the overall system was to be automatic, a digital computer would be used to provide correctly timed interrogation signals and to interpret returned information.
(3) As returning information was to be fed into the on-line computer, it was desirable to make the return path a digital link.

It was discovered in the early stages that very little was known about the behaviour of v.h.f. data links applied to vehicles moving in and around an urban environment. Therefore it became imperative to obtain statistical results using practical equipment, and a series of experiments were set up using the computer to gather and sort the necessary data.

Early experiments were conducted using audio-tone selective calling on the base-to-vehicle link. When a particular address was recognized the vehicle would reply to base with a 40 -baud message. Upon reception at the base station, this message would be de-serialized in the computer and the contents compared with a replica of the original message. If incorrect, details of this comparison would then be printed out and at the end of each run statistical data would be computed and printed (Fig. 3).

The experiments were organized in the following manner. Two complete sets of vehicle equipment were made available, each set comprising a two-way selective call f.m. radio and a specially developed digital generator which provided, on command, a pre-set message 16 bits in length. Each vehicle had a particular call sequence allocated to it, which the computer could select on a rotational basis, together with four sequences representing imaginary vehicles.

In the event of receiving no reply from a call to a genuine vehicle, the computer would break the rotational calling routine and recall the offending vehicle. If again no reply was received, a third call would
be made. If still no reply was forthcoming the legend NO REPLY would be printed out and the routine calling sequence resumed. Further, if after an interval of five minutes no reply at all had been received from a particular vehicle, it was assumed that a major failure had taken place and a visual indication would be given at base (Fig. 4).

After a great number of runs had been made with the vehicles operating over diverse routes covering both urban areas and open countryside, the considerable amount of data acquired was analysed and compared with similar results obtained using the radio equipment in voice communication surveys over the same routes.

The field pattern associated with v.h.f. radio installed in a vehicle operating within an urban environment is extremely complex and difficult to analyse. It can be


Fig. 4. Flow diagram for data link experiment.
visualized as a fixed pattern due to multiple reflections from stationary objects, buildings, street furniture, other vehicles, etc. On this is superimposed a continuously varying micro-structure due to traffic moving in the vicinity of the vehicle aerial. The situation is further complicated by the fact that the aerial is being caused to move in a somewhat erratic manner, due to traffic conditions, through this complex and changing pattern. The net result is that between vehicle and base there is an indeterminate transmission path, the characteristics of which change drastically from moment to moment. It has been shown that the field strength at the base receiver can vary as much as $20-30 \mathrm{~dB}$ at a rate dependent upon the speed of the vehicle and further modified by the relative presence and speed of surrounding traffic.

The transmission of voice over such a path generally causes little concern as the intelligibility of speech is not greatly affected by such rapid fading. But the very nature of digital data usually demands a near perfect transmission path. Additionally, the signal may fade during the 0.4 s time slot used for transmitting the 16 -bit message, with consequent corruption of data. However, in spite of this gloomy picture, the experiments showed that over a known good speech path in an urban area, data error rates of only a few per cent were likely. But even with error rates of this magnitude, data, to be usable, must be subjected to some form of error detection and subsequent correction.

## Obtaining navigational information

Having established provisional parameters of a mobile data link (b) the question remained, how could the necessary information be obtained and passed successfully over the link.

To solve the problem the vehicle requires some means which will enable it to determine its own position as outlined in (a). This is similar to the conditions imposed in conventional navigation and it would not be unreasonable to expect a solution to be obtained using the same approach. Indeed this approach is possible within the restraints of road traffic movements.

The classical method of navigation between two places requires several points, or 'fixes', to be taken along the route, where an accurate knowledge of actual position may be obtained. The number of fixes required depends on the accuracies of the results, distance between start point and destination, etc. Location between one fix and the next is determined by a


Fig. 5. T-junction as a three-port system.
(a)

(b)


Fig. 6. (a) Vehicle to base-location message, (b) base to vehicle-vehicle address message.
procedure known as 'dead reckoning', which is based on a knowledge of the direction and distance travelled from the last fix; consequently provision must be made for measuring this direction and the dis tance travelled.

It is of course possible to navigate entirely by dead reckoning. To be able to do so over large distances requires extremely accurate vector measurements with such expensive items as inertial platforms and on-board computers. However, the land vehicle operating in modes (b) or (c) is confined to a specific network of routes over which it is constrained to travel, and location systems can make use of these restraints.

By way of illustrating how such restrictions may be used, consider a $T$ road junction as a three port sub-system (Fig. 5). A vehicle $V$ entering at port $A$ must emerge at Port $B$ or $C$, or reverse out of port $A$, otherwise it must have stopped within the confines of the junction. In this example three detectors would be needed to cover the conditions of vehicle movement in areas between junctions.

Returning to the conventional method of dead reckoning with fixes, it is easily seen that such an approach can be made in a simpler manner in the road transport situation. All that is required to provide a system of vehicle location (i) to arrange within the vehicle a means of measuring distance travelled, (ii) to establish along each route a number of fixed points which, as each one is passed, may be identified by apparatus installed in the vehicle, and (iii) to determine whether or not the v.h.f. data link is adequate to pass this information to the central base station. It is, of course, assumed that the base station has data handling equipment available. This should be able to extract the necessary information from the link and display it in a form suitable for human operators to comprehend, thereby enabling control strategies to be applied.

## Wheel revolution counting

In a wheeled land vehicle a simple, if somewhat crude, method of measuring distance travelled is to count the number of revolutions made by the wheels while traversing a given route. Because this can be easily arranged in a modern motor car, experiments were planned in order to gain experience of this
form of measurement and to determine just how seriously data link I could be used in a practical system. To this end a suitably geared mechanical pick-off, operating a 10 -bit digital shaft-encoder, was fitted into the speedometer drive cable of one of the vehicles used in the previous experiments.

The equipment was so arranged that a call from the base station would initiate a reply from the vehicle containing an up-to-date indication of shaft-encoder position. Tone selective calling was used to address the vehicle but in this case each of the 16 bits of the reply message was given a different significance. The first three became a fixed start code, the next two were used as an indicator, followed by 10 bits of Gray code from the shaft-encoder, and the final bit was used 'as an end of message indicator (Fig. 6a).

Two routes were selected, both of which started and ended at the base station site. Route $A$ was about $3 \frac{1}{4}$ miles long mostly through lightly built-up areas. The longer route $B$, about $8 \frac{1}{2}$ miles, included a 4 -mile figure-of-eight loop in a heavily built-up town centre, situated about 3 miles from the base transmitter. A number of marker points, spaced one quarter to half a mile apart were chosen on each route and the vehicle crew was asked to throw a switch when passing each marker. The operation of the switch caused the two indicator bits in the message to change, signifying to the computer that such a point had been reached.

Several calibration runs were made and the information was stored in the computer. Operational runs were then performed, the results of which were printed out in the following form. A first column identified the marker points on the route. The second and third columns showed the times at which the vehicle reached the positions indicated in the first column. These were determined both by comparing the shaftencoder information with that obtained during the calibration run, and by a change in indicator bit condition. The fourth column indicated distance error and a fifth column provided some indication of average vehicle speed between markers. Statistical data on radio-link conditions during the run were collated at the end of each print-out.

Results showed that under good radio conditions adequate accuracies could be
achieved even with a simple set-up, position indications within 50 ft being frequently obtained, to some extent vindicating the wheel count method Tracking became difficult, if not impossible, with the simple system under bad radio conditions, i.e, heavy interference, shadowing, etc, indicating that, as had been expected, some form of error detection would be essential under such conditions.

As the system contained a computer it seemed natural to attempt a software solution to this problem. A vehicle tracking programme was written which enabled a number of credibility checks on the incoming data to be made and only those able to pass this screen were considered reliable. Tests with this programme gave very good tracking, even under quite heavy interference conditions, and it was felt that the feasibility of such a system for tracking route-plying vehicles had been demonstrated.

The next major step in this particular line of development was to improve the method of presenting results to a controller. It was therefore arranged to present the vehicle situation as a visual picture using a graphical display unit. It was logical to make use of this approach. as a computer was included in the system and flexibility of display afforded by this means made the case overwhelming. The opportuntity to be able to switch from a map of the area showing the immediate disposition of all his vehicles (Fig. 7) to another "presentation showing the up-to-the-minute operational situation on any particular route of his choosing gives the vehicle fleet operator a unique degree of operational control at the press of a button.

Clearly, the information that might flow over a vehicle-to-base digital link need not be restricted to positional data only. In fact it was arranged on certain occasions to make a change in message indicator bits to represent a 'driver alarm' signal. By this means the vehicle driver could alert a controller simply by throwing a switch in the vehicle, which caused a flashing alarm indication to appear on the controller's display screen. In a practical system a great variety of data could be sent back to base over the link. For instance, bus operation controllers might wish to know the passenger loading at certain times, and passengers could be counted automatically when boarding or alighting at bus stages, the information being relayed back to base.

## Data link II

The work so far had been done with only one, or sometimes two, vehicles. Because of the capital outlay required for such a system, it would only become really economic when applied to fleets containing probably a few hundred vehicles. This being so, some attempt had to be made to speed-up the calling rate of data link I which had been held to about one per second, for three reasons. These were, first, the use of tone-selective calling required 500 ms to achieve a successful


Fig. 7. Map display of the area showing the position of all vehicles.
interrogation, second, upon being called some time was needed for the vehicle transmitter to reach full power, and third, even a 16 -bit message took 400 ms to send at the 40 -baud rate. So a faster link-data link II-was considered.

The philosophy behind any system which might be produced was that of providing add-on digital equipment to any good commercially available mobile v.h.f. radio. In consequence it was felt that only the first or third items above could be tackled at this point in time. Indeed, by increasing the signalling rate to 1,000 bauds and providing a similar outgoing digital link for pulse code addressing, the interrogation and reply time would be substantially reduced. The next step therefore was to determine the feasibility of signalling over the link at this higher rate.

It was felt that the emphasis on the two main types of error would change when using 1,000 -baud rate, as opposed to 40 -baud signalling, due to the nature of the radio signal. The time required to transmit a complete message at the faster rate was less than that for just one bit at the slower, and this would manifest itself in a greater number of 'no replies' than 'corrupt messages'. Experiment largely confirmed this expectation, although there was a marginal increase in overall errors. However, it was established that there was no great penalty to be paid for using the increased data rate and work could now go ahead on providing a similar digital link from base to vehicle.

This entailed major changes in the hardware used so far at both ends of the link. For instance, the serializer in the vehicle had to be modified in order to
de-serialize the incoming message, and similar arrangements were required at the base end. Further, results had shown the need for some form of error detection for the outgoing link and this would now need to be accomplished by hardware methods in the vehicle. Some form of protection could be achieved by building a fair degree of redundancy into the interrogation message sent to the vehicle. For convenience, a 16-bit message was used but only 8 bits were made available for address purposes. A start code of four 'ONES' followed by a 'ZERO' preceded each address, which in turn was split into two blocks of 3 bits followed by a block of 2 bits, each block being punctuated by a 'ZERO' bit. A final 'ONE' acted as an end of message indicator as before (Fig. 6b).

A check was applied to incoming data at the vehicle end of the link to ensure that each message fitted into this format; if it did not the message was disregarded. A vehicle recognizing an address as its own would formulate a reply from the data contained at that moment in its data register and then transmit this back to base. Thus, as before, all that is required to complete a location system is to set suitably coded up-to-date vehicle position information in this register.

## Further navigational methods

Having already established that a simple wheel revolution counting system could be adequate for vehicles operating in mode (c), and that using a faster data link large fleets could be controlled, attention was turned to the more difficult problem of vehicles of the mode (b) type.

A clue to the solution to this problem might be found by returning to the subject of conventional navigation. So far we have explored the dead-reckoning approach and have found comfort in this for vehicles which are restricted to given routes. A little thought will show that this, combined with fixes arranged at strategic points within a given urban network, could provide a suitable location system.

Consider a vehicle which is operating in mode (b) travelling along a straight road in an ordinary town. Before very long it is likely to reach a crossroads and is presented with an element of choice. It may continue on past the junction or it may turn left or right; somehow the location system must determine which of these possibilities has been chosen. The system previously described, within limits, measures distance travelled, and it can be assumed that the base station has good knowledge of the town geography. Such a system can determine when a vehicle arrives at a particular junction but is unable to decide by which port it leaves. Some means must therefore be provided to overcome this dilemma.

As a first approach, a measurement of the degree of turn could be considered and, given sufficient accuracy, this method has a lot to recommend it. However, most practical methods of achieving this to the required degree of accuracy entail somewhat complex modifications to the mechanical parts of the vehicle. It is interesting to note that the principle of the ancient Chinese "southpointing chariot", which was chronicled some 5,000 years ago, provides one form of solution to this problem ${ }^{1.2}$. Further methods rely upon magnetic compass indication, but the presence of a large and variable number of oddly assorted metallic vehicles in the immediate vicinity rather precludes such an approach in this type of environment.

## Location systems using beacons

Another way of achieving the desired result is to provide a beacon at the side of each road leading away from the junction. If each beacon is uniquely coded and can be interrogated from the vehicle then, knowing the sites of each beacon, the base station is able to follow the progress of the vehicle. Again, if enough beacons are erected, one on each lamp-post perhaps, quite a good degree of positional accuracy may be obtained; sufficient for most practical purposes without the use of other methods such as wheel-revolution counting. This type of system bears a strong resemblance to railway 'block signalling', the position of each vehicle being determined by which block it is in at any time. The blocks in this case need be only a few tens of feet long.

Until recently the use of beacons was not considered to be particularly viable for vehicle location, the economics of such a system being most unfavourable. Some advant age had been gained elsewhere by using beacons in conjunction with wheel revolution counting for largely routeplying purposes. But the sheer number of
beacons required for mode (b) vehicles (several at each junction), even when combined with wheel revolution counting, demands a beacon which is cheap to produce, install, maintain and run. Although in the practical case a high initial cost may be defrayed to a considerable extent by a leasing agreement with other operators. For example, once installed, beacons could be used by police, bus and tram operators, taxis, delivery van fleets, etc. As such a system can easily be made mutually exclusive, the interference problem need not arise.

Beacons, and the way they are interrogated, may take various forms. The requirement is basically one of short-range communication and any of the standard methods from optics to ultrasonics can be used. The beacons themselves may beeither active or passive. Active beacons are those which continuously emit pre-coded information and the marine lighthouse is a common example of an active beacon. Passive beacons transmit their address signal only when triggered by some external source and may be further classified into two sub-groups, passiveactive and passive-passive, depending upon the method by which they are powered.

Passive-active types need some form of power to drive them even in the quiescent state. A radio beacon is usually of this form in that the receiver must remain on at all times, other than when the transmitter operates, in order to amplify and detect the triggering signal. For this purpose a source of external power is required. The wartime I.F.F. transponder is a practical example of this type of beacon.

Passive-passive beacons are completely inert, requiring no external power at all while waiting to be triggered. They derive the power which enables them to reply, solely from the external energy required to trigger them. For example, the rear reflector on a motor car needs no external power supply but emits a red-coded 'address' when triggered from a white-light source. Clearly, the advantages gained from using passive-passive beacons in a vehicle location system are considerable. No batteries or mains supply are needed so that installation and maintenance effort required are minimal and they cost nothing to run. At the present time the use of optics allows the most practical method of applying a passive-passive beacon solution to the vehicle location problem.

In one such system beacons consisting of horizontal reflective strips are illuminated by a vertical scanning beam emanating from the vehicle. The reflected reply is de-scanned, detected by a photo-cell, and after amplification provides an electrical analogue of the beacon code. This information is stored in a register until a demand is received over the v.h.f. data link, whereupon the beacon address is transmitted back to base. Knowing that the code is that of a particular beacon, and the beacon is situated in a certain place, the base station now has the exact position of the vehicle and can display this to the operator in some pre-arranged form.

Using optical passive-passive methods the beacons become purely reflective, and a first requirement is to devise some way of coding each beacon in order to give a unique reply. In the present system this is achieved by using strips of retro-reflective material. Retro-reflection is the property of a material to reflect a beam of light back along the axis of the incident beam. A ray of light incident on a plane reflecting surface is reflected at the same angle as that made by the incident beam to the normal, but on the opposite side of the normal. A plane surface is only retro-reflective to light reaching it along the normal.

Beacons could be coded digitally by using the presence of a strip to represent 'ONE' and no strip to represent 'ZERO', but this simple method is unsatisfactory for the following reasons. In practice a vehicle may pass a beacon at any distance across the car riageway, it may be travelling in the inside lane when interrogating one beacon but in the outside lane when passing the next. Therefore the beacon reading equipment must be able to read and store the beacon information at distances ranging from a few feet to a few tens of feet. This means that the frequency and pulse width of a reply can vary considerably in the practical case, because the angle subtended by the beacon alters with distance from the reading head.

Further difficulties occur due to a difference in the installed heights of various reading heads. Clearly, for a system to be practicable it must accommodate reading equipment which can be fitted on the roof of a Mini or on top of a double-deck bus. In this respect too it is most desirable to allow a wide tolerance on the installation height of the beacons themselves. For these reasons the beacons must be capable of being read at a variety of vertical angles and the reading equipment must be able to extract the beacon code under these conditions. This possibility of a slant presentation results in a further change in pulse width and frequency during a single scan, but both these difficulties can be overcome by devising a method of extracting both timing and code information from the reply signal.

Modulation of the light beam by frequency shift (two colour), polarization, or pulse-width techniques afford ways of deriving the required information, and both methods have been used in the system under consideration. But before discussing these methods in greater depth some thought must be given to how the beacon is to be read.

As previously mentioned, the beacon is scanned vertically. The light source needs to supply an extremely well collimated beam, one which can project a spot of less than about $\frac{1}{4}$-in diameter at a distance of about 40 feet. This is a very exacting requirement but one which can be readily met by using a low-power laser. The monochromatic property of the laser, used together with suitable filtering, also provides a considerable signal-to-noise advantage. The beam is deflected on to an eight-sided mirror-drum which rotates at
about 2,500 r.p.m., thereby scanning any beacon in its path. The need for retro-reflection now becomes clear, the return signal so formed is de-scanned by the mirror-drum and deflected on to the sensitive area of a photo-diode (Fig. 8). This is all the optics required for the pulse-width coded beacon as the necessary information can be extracted from the photo-diode output electronically, and we are now able to consider the operation of this system in greater detail.

Width-coded beacons (Fig. 9a) are divided into $1 \frac{1}{2}$ in horizontal zones, the first inch of a 'ONE' zone and the first half-inch of a 'ZERO' zone consist of reflective material (Fig. 10a). The signal received from such a beacon is of the form shown in Fig. 10b, and this is used to gate an up-and-down counter which normally counts a faster-running pulse signal. A positive-going edge causes the counter to count up until a negative-going edge reverses the count. The state of the counter is $r$ ead out at each positive edge and if it contains a positive number the appropriate register position is written to 'ONE' if negative a 'ZERO' is written. Immediately after reading the counter is reset ready for the next signal bit. This process is shown diagrammatically in Fig. 10c. marked A.


Fig. 8. Basic optical system.


Fig. 9. (a) Width-coded beacon and (b) beacon for polarized light method.
Beacons for the polarized light method consist of alternate equal width strips of reflective and non-reflective material (Fig. 9b). Coding is achieved by covering certain reflective strips with polarizing material and the whole beacon is scanned by a beam of polarized light. This causes a rotation of direction of polarization to occur on light returning from the covered strips while no change occurs on the uncovered ones. By splitting the returned beam after de-scanning, and passing each split beam through suitably arranged polarizing filters, the output of one of the two photo-cells detecting these signals will

(a)

(c)

Fig. 10. (a) Width-coded beacon, (b) width-coded beacon waveform, and (c) the counting operation of up/down counter. The counter is read and then reset at points
contain information from each strip, and the other only that from the polarized strips. The signal from the second cell may therefore be clocked into the register using the output from the first cell as a strobing signal.

All estimates existing today predict a continued rise in the number of road vehicles over the next 50 years. In Britain alone this number is expected to top 35 millions. With this order of density it becomes transparently clear that the present "Brownian motion" of traffic can no longer be toler ated and orderly control will have to be applied to a greater extent.
Over the past year several small location systems have been demonstrated. Wheel revolution counting, polarized and widthcoded beacon methods have been shown in an attempt to illustrate that solutions do exist to the somewhat difficult problem of vehicle location. The first faltering steps have been taken into the realms of practicability, and it is not unreasonable to suppose that great strides will now be made in this particular subject.

## References

1 ''Differential Gears" by Ernest F. Carter, Design and Components in Engineering, 9th February 1967.
2 "The History of Marine Navigation", by Per Collinder (translated by Maurice Michael), Batsford 1954.

## Letters to the Editor

The Editor does not necessarily endorse opinions expressed by his correspondents

## Electronics in medicine

In expressing my support for the editorial "Electronics in Medicine-the Future" in the June issue, I should like to draw attention to an underlying handicap retarding the development of biomedical engineering technology in the United Kingdom.

Medical electronics is a branch of biomedical engineering, a multidisciplinary scientific activity. In 1958 , following the initiative of Dr. Zworykin, the first of the International Conferences on Medical Electronics was held in which many kinds of specialists from the life and basic sciences have contributed. In hospitals of the National Health Service and Medical Faculties of the Universities, where direct collaboration between medical and engineering personnel is possible and desirable, there is still no recruiting, training or career structure for chartered engineers. Is it merely a rhetorical question to ask how the engineering side of biomedical engineering can be carried out without the participation of professional engineers?

Some hospital physicists, aware of the need for engineering in the medical environment, have retrained themselves as engineers. The situation in the universities is even less satisfactory, for the normal staffing structure in an electronics laboratory is the "one- (or two-) man-band", each one organized independently, one or more to a department according to the demand. There is no need to emphasize the consequent duplication of capital outlay and failure to utilize available skill.

It appears to the writer that the engineer is not yet accepted in biomedical engineering, and that non-engineers do not understand either the need for engineers, or the work they do. The remedy, of necessity, must originate from within the engineering profession. The initiative must be both practical and independent of external support or patronage. Only when engineers, as a profession, are making an indispensable contribution to the inter-disciplinary cause, also providing training and research facilities, will the engineer be welcomed by non-engineers. Five years ago, Dr. Zworykin proposed the setting-up of an Institute of Biomedical

Engineering. May $I$ as an engineer, propose that the Council of Engineering Institutions give consideration and support for the creation of such an institute?
R. E. GEORGE,

Physics Dept.,
Medical School,
Guy's Hospital, London S.E.1.
Your editorial in the June issue rightly draws attention to the difficulties faced by companies manufacturing medical electronic equipment, especially for the U.K. market. In it you suggest that equipment produced for the general user has potential applications in medicine, but the converse is just as of ten true.

The evolution of electronics from radio began before the incentive of war-time radar, helped greatly by physiologists and associates who asked for the impossible. and then provided it themselves. For example, between the wars, Matthews, Offner, Tonnies, Schmitt and others transformed the crude audio amplifier by adding differential inputs, increasing gain and stability, and extending the frequency response towards zero. Since the war, medical workers have been constantly breathing down the necks of solid-state designers, demanding higher input impedances, less noise and many other characteristics that have proved invaluable elsewhere.

It is not only in the fields of circuit techniques and components that biomedical engineering (as it is now known) has influenced electronics in general. Many items of hardware developed specifically for medicine have found other applications, perhaps after minor modifications.

This company manufactures a patient monitoring system that has evolved from initial work in a medical research establishment, but the specially developed indicators and chart printers are now proving to be of a great interest to instrumentation and control engineers in many industries. By exploiting this greatly extended market, it is possible to provide the hospitals with what they want at a price the nation can afford.
ANTHONY S. VElate,
T.E.M. Engineering Ltd,

Crawley, Sussex.

## Rationalizing trade associations

I was most interested in the editorial in your issue for July because a rationalization of the many trade associations in the electronics field is long overdue.

In 1956 I was appointed secretary of R.C.E.E.A.-now E.E.A.-and a year later I put up a scheme (which would probably have led to my immediate retirement) for the administration of all these associations within the general confines of the British Electrical and Allied Manufacturers' Association. I learnt very quickly that this was a non-starter at that time, although the economic factors and almost entirely common membership of E.E.A. with B.E.A.M.A. made it a logical development.

There were two reasons why it was not acceptable then. One you have high-lighted. That is the reluctance of some associations (or their council members) to surrender their autonomy. The second was never publicly recorded, but was, the intense jealousy between member companies, which led them to believe that their own interests were more important than those of the industry, or indeed of the nation. I am convinced that the latter has been the real reason why no rationalization of the electronics industry representation has so far taken place.

However, the last few years have seen a major re-grouping of the companies in this field, and there are consequently fewer heads of businesses to be convinced of the obvious economies to be achieved by ending the proliferation. One would therefore hope that the rationalization of the trade associations, which the E.E.A. is apparently trying to achieve, will go forward. The resulting benefits to the nation should in the long term benefit the member companies also.

The top men who would comprise the "voice that could speak to governments, other associations and foreign organizations" are unlikely to have the time to do it in B.E.A.M.A. and E.E.A. etc. Perhaps after thirteen years the jealousies are becoming less pronounced, and the powerful voice may yet emerge.
H. E. F. Taylor,

Torquay,
Devon.

## Mobile radio and amateur bands

In your issue of July 1970 you quote from the recently published Annual Report (1969) of the Electronic Engineering Association: "The lack of spectrum space continues to be seen as the most likely factor which could seriously limit the expansion of mobile radio communications. Negotiations have therefore now begun with the Ministry of Posts and Telecommunications to secure the use of the 68 to 71.5 MHz and 420 to 450 MHz bands."

The reason why our Association has suggested to the Ministry of Posts and

Telecommunications that 68 to 71.5 MHz should be made available to mobile radio communications arose from the recent announcement that the GEE navigational chain which operated in that band had closed down. In making the recommendation I do not think that any of our members were aware that this part of the frequency spectrum was used by amateurs. Indeed, it seems that the allocation was made without the usual formality, and only upon a noninterference basis.

In regard to the $420-450 \mathrm{MHz}$ band, I feel sure that the amateurs will understand our concern as an industry that substantial frequency space, without which mobile radio cannot expand, is being made available above 470 MHz in the United States and below 450 MHz on the Continent. Mobile radio activity and the size of the industry it can support, and the amount of research and development that the industry can support, are in the last analysis dependent upon the adequate availability of frequencies. If the problem of expansion in the all important u.h.f. sector is not solved then leadership in product development and export will undoubtedly pass from Britain to those industrial countries who are now receiving generous new allocations. It is against this background that our members question whether the country can afford, even on a non-interference basis, the allocation of 22 MHz to amateur television.

Our members have the highest regard for amateur activities including their brilliant pioneer work above 1.5 MHz nearly fifty years ago, and would not wish to see them deprived of all facilities in the u.h.f. bands. We should welcome discussion on the subject with representatives of amateur associations. R. A. Villiers,

The Electronic Engineering Assoc.,
London, W.I.

## Class AB-some questions

Following the two articles on a class $A B$ amplifier design by Mr. Linsley Hood and also the correspondence in the August issue, we would like to raise several points concerning the specification.
Total harmonic distortion is specified as less than $0.02 \%$ at all power levels below maximum output, but this is presumably (see Figs. 6 and 7) only at 1 kHz though not specified as such. What are the distortion levels at 100 Hz and 10 kHz at full output, for example?

When quoting a noise level for the amplifier, the noise bandwidth of the measurement was unspecified thus rendering the result as meaningless as quoting a frequency response without limits (e.g. $\pm 3 \mathrm{~dB}$ ).

A value for "square-wave transfer distortion" is given as $0.2 \%$ at 10 kHz but the power level is not specified. As "square-wave transfer distortion" is a non-standard quantitative measurement, for the result to be meaningful, an explanation is required as pointed out by Mr. Gibbs in his letter in the August issue.

Also results for other amplifiers, for example a good class $B$ amplifier, would be useful for comparison.
Martin Smith and
H. P. Walker,

Southampton, Hants.

Notwithstanding the perfection of Mr . Linsley Hood's latest amplifier in practice, I would differ with him over some of the points he raises in the July issue.

A Darlington pair has a lower mutual conductance than the output transistor on its own. The converse can only be true of the complementary pair configuration. His first paragraph attributes a higher value to both pairs.

The overall linearity of the output stage of his Fig. 2, when driven from a genuinely low source impedance, does depend on the quiescent current contrary to his expectations. A high drive impedance is the answer, with a low inter-base impedance. This does not impair the cut-off performance as the conducting transistor presents a low base-emitter impedance to the one being cut off.

The output stage of Fig. 3 operates between the common emitter and the common collector modes. The true emitter follower of Fig. 2 has an inherent distortion of about 100 times less than Fig. 3, provided that the source impedance is low enough and the quiescent current is appropriate. Infinite values of bootstrap capacitance are necessary to secure pure common emitter operation; this circuit is predominantly common emitter above 30 Hz . His calculation of class A output power assumes that the output transistors have a constant mutual conductance. Due to the bend in this characteristic at low collector currents they do not cut off as soon as expected. The class A output of either version is nearly $2 \mathrm{amps} \mathrm{pk}-\mathrm{pk}$. Using a standing current of 100 mA and no emitter resistors, a class A output of over $5 \mathrm{amps} \mathrm{pk}-\mathrm{pk}$ is available. (The traditional definition of class A does not preclude current ratios between the two halves of $10^{8}$.)
A high class A power is not, ipso facto, a particular virtue. The correct quiescent current is related to the linearity of the output stage under dynamic conditions, and this ought to be significantly lower than that required by full class $A$ operation, in a good class AB design.

The mutual conductance of MJ $481 / 491$ with 0.82 -ohm emitter resistors is 1 mho at high currents; this falls to 0.5 mho at a collector current of around 20 mA . If $\operatorname{Tr}_{3}, 4$, have high current gains, so that the drive impedance really is low, this is the optimum quiescent current with a bandwidth of a few kHz . Higher quiescent currents worsen the performance. A current of 200 mA is undoubtedly right for bandwidths greater than this, but no compromise would be necessary if the drive impedance was high enough for all combinations of transistors.

Poor matching of the output transistors is extremely unlikely to cause any noticeable deterioration of the performance, except to a distortion meter; low
gains may even be advantageous in certain cases. Full class A operation is unnecessary in both these circumstances.

My final point concerns the avoidance of temperature-compensation in the biasing of the output stage. The penalty for this is very poor thermal stability in the 8 -ohm version.
D. L. D. Mitchell, University of Bradford.

## I.Cs in stereo pre-amplifiers

We were very interested in the article in July 1970, by L. Nelson-Jones, describing an application of the RCA CA3048 as a stereo pre-amplifier.

The original RCA stereo pre-amplifier circuit was intended for use in low-cost applications and had a few sho:tcomings as observed by Mr. Nelson-Jones. A later RCA report published in June 1969 (A Monolithic Integrated Circuit for Stereo Pre-amplifiers, by L. Kaplan) describes several circuits which produce comparable performance to the circuit described by Mr. Nelson-Jones but use passive tone controls. The problem of signal-to-noise ratio was overcome by increasing the loop gain of the first pre-amplifier whilst still maintaining adequate overload capability.

The CA3052 is capable of producing a similar noise performance to the CA3048 when used as a stereo pre-amplifier provided amplifiers A2 and A3 are used for the magnetic inputs. These amplifiers are tested in production for equivalent input noise with full R.I.A.A. compensation, and amplifiers A1 and A4 are checked with a simple ' $C$ ' filter connected at the output. We should be happy to provide any further applications information to interested readers.

## L. R. Avery,

RCA Ltd,
Sunbury-on-Thames,
Middx.

## Jupiter probe

In the feature "News of the Month" in your August issue under the heading "Space Probe to Jupiter" you state that "This planet is believed to be the only one in our solar system which radiates more energy than it absorbs from the sun, current measurements indicating about twice as much." This is not true as all planets containing any radioactive material must radiate more energy than they absorb from the sun. No other planet, however, radiates as large an excess as Jupiter.

A planet must radiate enough energy to maintain its thermal equilibrium, and it is reasonable to assume that any planet will contain some radioactive core material, the decay of which will produce heat energy. It is evident, therefore, that to maintain thermal equilibrium a planet must radiate as much more energy than it absorbs from the sun as it generates itself in internal radioactive decay.
James M. Bryant,
Cheltenham, Glos.

# Transistor Breakdown-voltage Meter 

# Constructional details of a useful instrument which provides direct reading of junction breakdown voltage at fixed reverse currents 

by Jens Langvad*, M.Sc. (Danish)

Designers of power amplifiers, power supplies or any equipment using transistors working at high supply voltages often require to know the actual breakdown voltage of the transistors. The instrument described here was designed to replace the conventional method of just increasing the voltage slowly to see what happens.

The maximum collector-to-emitter or collector-to-base voltage specified by the transistor manufacturer is often grossly understated. This leads the circuit designer into buying expensive high-voltage transistors in cases where a standard type may do the same job just as well. The cheap BC107, for instance, usually exhibits a collector-to-base breakdown voltage [ $V_{(B R) C B O}$ ] in excess of 80 V , although the stated maximum operating voltage is only 45 V .

The reason for this is that in the planar manufacturing process it is not easy to keep the $V_{(B R)}$ within narrow limits. By stating a $V_{(B R)}$ well below the production average, but still above the need of most customers, allowance is made for a greater number of freaks and a lower rejection factor.

## Breakdown characteristics

For an ordinary silicon planar junction transistor three breakdown characteristics are of interest. These are: (1) the $V_{(B R) E B O}$, (2) the $V_{(B R) C B O}$ and (3) the $V_{(B R) C E O}$ voltage-current curves. (In accordance with accepted terminology the " $O$ " stands for open and refers to the third terminal.) The first is quickly dealt with; the $E B$ junction breaks down like an avalanche zener diode with a knee voltage of $6-12 \mathrm{~V}$, according to type (most BC 107s lie quite accurately at 8 V ).

The $C B$ diode breaks down in a similar manner, but the knee voltage is much higher. The $V_{(B R) C B O}$ is the most important of the three, as it determines the maximum peak-to-peak collector voltage swing one can expect from the transistor.

The CEO characteristic is shown in Fig. 1 together with the $C B O$. (There is no scale factor, as this depends entirely on the type of transistor investigated.) At very low currents the two curves are seen to coincide, but after reaching the knee the $V_{(B R) C E O}$ drops with increasing current, thus exhibit-

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Fig.1. Typical breakdown characteristics.


Fig.2. Principle of breakdown-voltage meter.
ing a negative resistance characteristic. If, however, an external resistance is present between the base and the emitter the $C E$ curve approaches that of the $C B$. If, for a low-level transistor, $R_{B E}$ is less than $100 \mathrm{k} \Omega$ (and this will be the case in most amplifier applications) the two curves may be considered as coinciding.

## Breakdown-voltage meter

The breakdown-voltage meter itself comprises a simple d.c. supply giving the unusually high output voltage of 200 V , in connection with a current limiter covering the equally unusual range of $0.1 \mu \mathrm{~A}-1 \mathrm{~mA}$ in decade steps. In Fig. 2, $T r_{1}$ and $T r_{2}$ are high-voltage type transistors. $A$ is a differential input amplifier working as a voltage comparator and $E$ is a reference voltage. When no current flows in the test object the output of $A$ is zero, so that $T r_{2}$ is cut off and the series transistor $\operatorname{Tr}_{1}$ saturated through $R_{1}$. When the test object is connected, the current flowing through it will produce a voltage drop across $R_{2}$. This
voltage cannot exceed $E$, because if it did, the voltage comparator would turn over, saturate $T r_{2}$ and thus drive the supply voltage towards zero.

Provided that the input impedance of $A$ is much greater than $R_{2}$, the current in the test object is seen to be limited to $I=E / R_{2}$. Thus $I=1 \mu \mathrm{~A}$ and $E=0.5 \mathrm{~V}$ require $R_{2}=$ $0.5 \mathrm{M} \Omega$. The voltmeter $V$ indicates the voltage required to drive $I$ through the test object, plus the reference voltage $E$. But the latter is small enough to be neglected.

## Practical circuit

The complete circuit diagram is shown in Fig. 3. Any transformer giving 200-250V and 6.3 V may be used. The zener-stabilized low voltage supplies the voltage comparator and also works as a reference for the voltage limiter. (This is of the usual kind and serves only to limit the maximum voltage to full scale deflection on the meter.) There are two voltage ranges: $0-100$ and $0-200 \mathrm{~V}$, and the voltage divider for the limiter and the pad for the meter are switched simultaneously by $S_{1}$. Transistors $T r_{1}, T r_{2}$ and $T r_{3}$ are high-voltage devices, RCA type 2N440, but any type with a $V_{(B R) C B O}$ of 300 V or more would do.

Transistors $T r_{4}, T r_{5}$ and $T r_{6}$ constitute the voltage comparator. The f.e.t. input transistor provides the amplifier with an input impedance approaching infinity. The diode-resistor network in the input protects the f.e.t. against voltage surges. $S_{2}$ selects the current ranges $0.1 \mu \mathrm{~A}-1 \mathrm{~mA}$. The selected value of current obviously depends on the type of transistor under test, but usually the $V_{(B R) C B O}$ is remarkably independent of the current at which it is measured. Generally speaking, one should use the low-current ranges for low-level planar transistors, and the two highest ranges for germanium or power devices. When measuring $V_{(B R) C E O}$ one can get a fair impression of the shape of the breakdown characteristic just by rotating $S_{2}$.
$S_{3}$ switches between positive and negative supply for $\mathrm{n}-\mathrm{p}-\mathrm{n}$ and $\mathrm{p}-\mathrm{n}-\mathrm{p}$ transistors respectively, and $S_{4}$ connects the transistor either $C B O$ or $C E O$. In the midposition the transistor is disconnected and the supply voltage turned down. This is achieved by $S_{4 C}$ shorting the base of $T r_{1}$ to ground. $S_{4}$ could be a keyswitch biased in both directions, so as to ensure that the

switch is always in the neutral position when the transistor is inserted. When $S_{4}$ is operated, the voltage does not jump but rises fairly slowly owing to the $10 \mathrm{k} \Omega / 16 \mu \mathrm{~F}$ $R C$ network. This is necessary in order to avoid dangerous current surges in the test object.

The test current may be adjusted by altering the base voltage of $\operatorname{Tr}_{5}$. It is easily set to the correct value by means of a known resistor. With $470 \mathrm{k} \Omega$ connected between $C$ and $B$ terminals, $S_{4}$ in position $C B$ and $S_{2}$ in position $100 \mu \mathrm{~A}, P_{1}$ should be adjusted until the meter reads 47 V . $(100 \mu \mathrm{~A} \times 470 \mathrm{k} \Omega$ $=47 \mathrm{~V}$ ). In this context it can be mentioned that the instrument is ideal as a megohmmeter, having a linear scale and covering a range of 0.1 to $2000 \mathrm{M} \Omega$ f.s.d.

Mounting of the components is far from critical; yet it is recommended to put the whole in a closed metal box and connect this to circuit earth so as to avoid the disturbing influence of hum voltages on the high impedance input. However, insulate the box externally (a coat of paint may suffice), or be very careful with external test-leads, as a short from either of the connecting terminals to the case will prove fatal for at least half of the transistors.

If the components are mounted on a printed circuit board, trouble might be experienced with the low current ranges owing to stray currents on the board. This can be countered by keeping the gate of the f.e.t. and associated leads and components on a "stand-off", away from the etched side of the board.

## A Quick Look at Display Devices

Information present inside a piece of equipment-be it a computer, a measuring instrument or what have you-is of no use unless it can be made to do something or it can be presented to the outside world in a way that can be understood by human beings.

Ordinary incandescent lamps can be used individually to show simple on-off or yes-no information or they can be used to illuminate a more complex legend, "No. 3 alternator failure", for instance. Early counter-timers used such lamps to illuminate the digits 0 to 9 either by edge-lighting perspex sheets or by illuminating an engraved or printed window. However the flexibility is limited and the current consumption is high, and most of the power consumed is wasted as heat.

Some of the above remarks apply to simple neon indicators, but here, low brightness and high-voltage replace the high-current and heat disadvantages.

Gas-filled indicators, such as the Nixie, have long reigned supreme in the instrumentation field where a numeric only readout is required but they are of no use when letters and words have to be displayed.
The cathode-ray tube is now much used to display alphanumeric information and the methods of doing so are as varied as they are numerous. Character generators for c.r.ts can now be purchased in integrated circuit form which use the seven-segment method of presentation. Seven lines are generated which can be used to assemble all the numbers from 0 to 9 plus a few letters. More complex electronics can be employed to produce on a
c.r.t. upper and lower case alphabets, all the numerals and a varied assortment of symbols. Although expensive with complex scanning, blanking, decoding, addressing and storage circuitry this type of display is much used, often in association with computers.

The single incandescent lamps and the neon lamps can be grouped together in a $5 \times 7$ matrix to provide a display capable of showing a full range of alphanumeric characters and symbols. The array of lamps in this case is driven by a logic net work which receives coded input information and determines which lamps have to be lit to display a given character. The same $5 \times 7$ matrix approach can be, and is, used with c.r.ts, here the matrix is formed by dots on the tube face.

The latest contender in the field of displays is the light emitting diode and our front cover this month shows an integrated array produced by Standard Telecommunication Laboratories Ltd which, as can be seen, is based on a $5 \times 7$ matrix. These lamps are forward biased diodes which emit a narrow band of light by the recombination of injected holes and electrons across the energy band gap of a single crystal material. The diodes are manufactured from a mixture of gallium phosphide and gallium arsenide. They have the advantage of requiring voltages and currents that are compatible with those normally found in transistor and integrated circuitry.
Another display medium which we will be hearing a lot about in the future is liquid crystal; a substance which can be held in a layer between two transparent surfaces and turns opaque when an electric field is applied.

## Active Filters

# 13. Applications of the active-ladder synthesis 

by F.E. J. Girling* and E. F. Good*

The application of the active-ladder synthesis to low-pass and high-pass filters with and without zeros in the stop band, and to simple band-pass filters is discussed.

## Butterworth ladder filters

Because only moderate $Q$ factors are needed, Butterworth responses are in general suitable for realisation by factors. Nevertheless, by misalignment of the factors
(a)

(b)

(c)

(d)

(e)

(f)


Fig. 1. Butterworth ladder fitters normalised for $\omega_{c}=1 \mathrm{rad} / \mathrm{s}$.
on the frequency axis or by errors in $Q$ factor, an appreciable slope can be introduced into the pass-band response by component errors which would cause very little change in pass-band response in an equally terminated filter (much as in the example shown in Fig. 3 of Part 12).
Now although Butterworth responses have relatively rounded corners, over much of the pass band they show a high degree of flatness, e.g. Sth-order response is $1 \%$ down from the zero-frequency level at about 0.85 of $\omega_{c}$. If this degree of flatness is to be achieved in practice, therefore, without calling for a tight tolerance on the values of the reactances (or their equivalents in an active filter, the values of the $T \mathrm{~s}-$ or $C R$ products), an equally terminated ladder filter is the preferable choice. Diagrams for orders 2 to 7 are shown in Fig. 1 (although the filters of orders 2 and 3 do not really come within the scope of the present argument) and it is interesting to notice that the normalised reactance values coincide with the reciprocals of the $Q$ factors (Part 9, table 6).
The theoretical structure for a 5 th-order active ladder has already been given (Fig. 13(d) of Part 12) and may be turned into practical form as in Fig. 2 herewith. In this diagram the inverting stages have been moved to new positions to reduce the number of resistors connected to the second and fourth integrators.

If the frequency response is compared with that of the 5 th-order constant- $k$ filter, Fig. 6, it is seen that the shapes are little different, except that the constant-k filter gives a more rapid fall into the cut-off region. When normalised for -3 dB at I radian/second the element values of the constant- $k$ filter are as given in Fig. 3, and
comparison with those of the Butterworth filter give an indication of the tolerances allowable without losing flatness in the pass band or attenuation in the stop band.

In a filter such as that shown in Fig. 2, if $R_{\text {in }}=R_{5}$ the voltage gain is the same as that of the passive model, $\frac{1}{2}=-6 \mathrm{~dB}$. There is no necessity to stick to this figure, however. First $R_{\text {in }}$ may be varied over a considerable range. Secondly the gain of any stage in the forward path may be changed provided the gain of the surrounding backward path or paths is/are changed in inverse ratio. Thus the signal level at the output may be raised without altering the shape of the response curve by reducing $R_{1}$ and increasing the lowest-positioned of the three resistors $R^{\prime}$ by the same ratio; by reducing $R_{2}$ and increasing the already mentioned resistor marked $R^{\prime}$ and the lower of the two resistors marked $R_{3}$; etcetera. Such changes assume, of course, that each affected amplifier has sufficiently high internal gain to behave still sensibly ideally.
As the first and last integrators have a feedback resistor connected across the capacitor, they provide in effect a simple lag and an unwanted sign change. More economical ends may be used, therefore, as shown in


Fig. 3. Constant-k filter normalised for $-3 d B$ relative to zero-frequency level at $1 \mathrm{rad} / \mathrm{s}$.

Fig. 4. These are lag and integrator circuits (Part 5) and they replace the end two integrator loops of the basic active ladder. The input resistor is now part of a time constant and so cannot be varied independently. Other means of varying the overall gain remain, however.

For a sharper corner and increased attenuation in the stop band Chebyshev filters may be used, and element values may be taken from reference works (e.g. Ref. 1). There is also something to be said for taking as a model a "classical" constant- $k$ filter.

## Constant- $k$ filters

Constant- $k$ or $A$-type filters (Ref. 2) have attractive regularity, Fig. 5, which allows all the integrators of the active ladder to have the same $T$ (except the end ones, which are of half value). When the central elements
*Royal Radar Establishment

for $\omega_{C}=\mathrm{rrad} / \mathrm{s}$
$T_{1}=C_{1} R_{1}=0.618 ; T_{2}=1.618 ; T_{3}=2 ; \quad T_{4}=1.618 ; T_{5}=0.618 ; R^{\prime}, R^{\prime \prime}$, and Rin orbitrary

Fig. 2. Active 5th order Butterworth filter modelled on Fig. 1(d).
of the passive models are designated $2 L$ and $2 C$, as shown, the nominal cutoff frequency is given by

$$
\begin{equation*}
\omega_{n}=1 / \sqrt{ }(L C)=1 / T \text { (say). } \tag{1}
\end{equation*}
$$

Hence, since $R=\sqrt{ }(L / C), L / R=C R=T$. In the basic active ladder, therefore, all the integrators have $C R$ products equal to $2 T$, except the end ones which have value $T$.

From the responses shown in Fig. 6 it can be seen that these filters are not of equal-ripple type. They are not, therefore, optimum designs: a Chebyshev filter of equal order and with the same maximum

- depth of ripple in the pass band gives a steeper initial fall into the cutoff region, though the ultimate rate of fall is necessarily the same; or alternatively for the same steepness of initial fall the Chebyshev filter gives a smaller maximum depth of ripple.

The 3rd-order filter is identical with a Butterworth filter; the high-frequency and low-frequency asymptotes intersect at the nominal cutoff frequency, and $\omega_{n}=\omega_{c}$ (the

> (a)
$T_{2}=L / R, T_{1}=C R$

$$
T_{2}=C R, T_{1}=L / R
$$


$C_{2} R_{2}=T_{2}, C_{1} R_{1}=T_{1}$
(b)


$$
T_{m}=C_{m} R, T_{l}=C_{l} R
$$

Fig. 4. Methods of making economical ends.
(a)

(b)

(c)


Fig. 5. Constant-k low-pass ladders.
-3 dB frequency). As the order increases, an increasing proportion of the reactances (or integrators) have the value 2 , and the high-frequency asymptote moves down the frequency scale. This causes the initial fall into the cutoff region to be steeper than the asymptote: for the 5 th-order about $35 \mathrm{~dB} /$ octave, compared with $30 \mathrm{~dB} /$ octave; for the 7th-order about $60 \mathrm{~dB} /$ octave, compared with 42 ; for the 9 th-order about $90 \mathrm{~dB} /$ octave, compared with 54 . By the 9 th-order a pronounced and unpleasant ripple has appeared towards the end of the pass band; but up to the 7th-order the amplitude response is quite good enough for many purposes, and the fact that the integrators can be made up using a number of resistors all of one value, and a number of capacitors also all of one value, can make these filters a convenient choice in experimental work.
Also shown in Fig. 6 are curves for the voltage at the output of the centre integrator, which is the replica of the voltage across the centre capacitor (if there is one) of the passive model, or of the current through the centre inductor. These show an increasingly large resonant peak as the order increases. This means that the centre integrator could overload before full output is reached at the final integrator. This possibility can be avoided, however, by increasing the forward gain of one or more of the loops at the output end of the filter and reducing the gain of the feedback parts of the loops as already described.
Some peaking occurs at the centre of Butterworth filters, but to a less degree as they are less resonant. This can be seen by comparing the $Q$ factors of a Butterworth filter (Part 9, Table 6) with those of a resist-ance-terminated constant- $k$ filter given herewith (Table 1). The high $Q$ factors are, of course, the price paid for the steeper initial cutoff, and if the integrators do not have high zero-frequency gain this will show as
an imperfection in the realised response more than with a Butterworth filter.

## Effect of finite gain

In a realisation by factors it is easy to estimate the effect of finite gain and make correction by adjusting element values (provided more than the minimum necessary


Fig. 6. Constant-k filters: output voltage and voltage at centre. (a) 5th order; (b) 7th order; (c) 9th order.
gain is available)-see Part 9. In a ladder it is a straightforward matter to calculate the effect of finite gain in an integrator, which as shown in Part 7 is equivalent to finite $Q$ in the corresponding reactance. But when the model is an equally terminated filter, and all but the reactances should be of infinite $Q$, no adjustment of element values can compensate for finite $Q$ in these reactances or finite gain in the corresponding integrators. In the active ladder, the loss may be compensated by raising the effective amplifier gain to infinity by positive feedback. This may be applied through a sign inverting amplifier, as shown in Fig. 7; or


Fig. 7. A method of applying positive feedback to compensate for finite gain in an integrator.
if a differential input terminal can be found (e.g. the emitter of the input transistor) the positive feedback may be applied directly over the integrating amplifier. What is aimed at is that each of the inner resonant loops when freed of loading from the rest of the filter should have infinite $Q$, and in practice it is sufficient to apply positivefeedback correction of approximately double magnitude to only one integrator of each loop. It need hardly be said, however, that nowadays the best course of action, at any rate for a low-frequency filter, is to use an operational amplifier of ample intrinsic gain so that no compensation is needed. It should, of course, not be forgotten that capacitors do not have zero loss. But the availability of polystyrene capacitors showing $Q$ factors from 2000 to 5000 makes it unlikely that much difficulty will be experi-
enced on this score; and polycarbonate capacitors showing $Q$ factors of about 500 , and having the advantage of much greater compactness in capacitances of $0.1 \mu \mathrm{~F}$ and over, are usually quite satisfactory.

The effect of finite amplifier gain in distorting the pass-band response is shown by some experimental results obtained by the present authors many years ago. At that time transistors were in a very primitive state, and the only sensible choice of amplifier seemed to be a single pentode valve, Fig. 8. With the loss in the coupling and mixing networks it is probable that the effective amplifier gain was 50 to 100 , and the measured response is shown in Fig. 9, curve (b). To increase the effect the valves were connected as triodes, giving an effective gain of probably 10 to 20 , and the result is shown in curve (c). The curves have been adjusted vertically for easy comparison, i.e. the extra zero-frequency loss is not shown, and it is clear the main effect is felt near the "pole" frequency of the highest- $Q$ factor and indicates a damping down of the $Q$ of that factor.

## Adding zeros in the stop band

The performance of a filter is often improved at small expense by adding zeros in the stop band, as mentioned in earlier parts; and in a passive low-pass ladder filter a zero is obtained if either (1) a series arm inductance is tuned with a parallel capacitance (so that, ideally, the impedance of the arm becomes infinite at the required frequency) or (2) a shunt arm capacitance is tuned by a series inductance (so that the impedance of the arm tends to zero at the required frequency). Strict correspondence between the internal working of the passive filter and an active counterpart would require an extra integrator for every added reactance. However, the present writers' colleague, Dr R. L. Ford, has shown that satisfactory results can be obtained by making some additional interconnections to the simple (all-pole) structure, in much the same manner as

Table 1. Factors of constant-k filters with resistance terminations for nominal cutoff frequency of $1 \mathrm{rad} / \mathrm{s}$.



Fig. 9. Responses of 7th-order low-pass active ladder filter: (a) theoretical, (b) measured using pentodes, (c) measured using triodes.
notch response can be obtained from a twointegrator loop (Part 7).
The basic idea is that in Fig 10, for example, the current in $C_{2}{ }^{\prime}$ is proportional to ( $p V_{3}-p V_{1}$ ) and therefore to ( $I_{3}-I_{1}$ ), the difference of two quantities which, at least potentially, are already available in counterpart in the active system. Hence the counterpart of the required difference ( $I_{3}-I_{1}$ ) can be formed and added with a suitable scaling factor to the counterpart of $I_{2}$ to represent the addition of $I_{2}{ }^{\prime}$ to $I_{2}$ without the use of any additional integrators (or differentiators). This is shown in Fig. 10(b). The additional links are $r_{1}$ and $r_{3}$, and their correct values relative to $r_{2}$ can be found by the following analysis.

In the passive network

$$
\begin{equation*}
I_{2}^{\prime} / p C_{2}^{\prime}=V_{2}=V_{3}-V_{1} \tag{2}
\end{equation*}
$$

so for the counterpart quantities in the active system we should have

$$
\begin{equation*}
I_{2}^{\prime} R=\left(V_{3}-V_{1}\right) p T_{2}^{\prime} \tag{3}
\end{equation*}
$$

where $T_{2}{ }^{\prime}=C_{2}{ }^{\prime} R, R$ being the scaling factor chosen for converting the currents of the passive network into voltages in the active system.
The voltages shown as available in Fig. 10(b) are

$$
I_{3} R=V_{3} p T_{3} \text { and } I_{1} R=V_{1} p T_{1} .
$$

$I_{2}{ }^{\prime} R$ may therefore be obtained by implementing the equation

$$
\begin{equation*}
I_{2}^{\prime} R=V_{3} p T_{3}\left(\frac{T_{2}{ }^{\prime}}{T_{3}}\right)-V_{1} p T_{1}\left(\frac{T_{2}{ }^{\prime}}{T_{1}}\right) . \tag{4}
\end{equation*}
$$



Fig. 8. Very early version of 7 th-order low-pass active ladder filter. $R=390 \mathrm{k} \Omega, C=1000 \mathrm{pF}, 2 \mathrm{C}=2,000 \mathrm{pF}, V_{1}-V_{10}=C V 138$.

Now for the system as shown in Fig. 10(b)

$$
\begin{align*}
V_{x}= & I_{2} R\left(\frac{r_{2}}{r_{2}}\right)+V_{3} p T_{3}\left(\frac{r_{2}}{r_{3}}\right) \\
& -V_{1} p T_{1}\left(\frac{r_{2}}{r_{1}}\right) \tag{5}
\end{align*}
$$



Fig. 10. A method of introducing a zero of transmission by adding only resistors.

So $V_{x}=I_{2} R+I_{2}{ }^{\prime} R$ as required if

$$
\begin{equation*}
\frac{r_{3}}{r_{2}}=\frac{T_{3}}{T_{2}^{\prime}} \text { and } \frac{r_{1}}{r_{2}}=\frac{T_{1}}{T_{2}^{\prime}} . \tag{6}
\end{equation*}
$$

In practice the synthesis must be modified somewhat, since $I_{3} R$, the quantity representing $I_{4}+\left(-I_{2}\right)$ (we suppose for a moment that $C_{2}{ }^{\prime}$ is not present) does not appear as a single voltage, the summation being done by giving the $T_{3}$ integrator two input resistors. This situation is met by providing two input resistors $r_{3}$ for the inverting amplifier, as shown in Fig. 10(c), and the same is done for $-I_{1} R$ as shown on the right-hand side of the diagram. The result at this stage is rather cumbersome. But two of the added resistors are in parallel with the feedback resistor $r_{2}$, so the system may be simplified as shown in Fig. 10(d), the resistor $r$ being made equal to the parallel combination of $r_{1}, r_{2}$ and $r_{3}$.
Fig. 11 illustrates how the method can be applied to reproduce a 5th-order filter with two added stop-band zeros. The parameters have been chosen to realise a Darlington characteristic of the same shape as that shown in Fig. 1 of Part 1, and used as an example in Part 9, but scaled to a lower frequency to set the first zero at 50 Hz . The required time constants, in milliseconds, are given in the table.

## Variable tuning

The filter shown in Fig. 11 also serves to illustrate how variable tuning may be applied. The requirement is to vary the $T \mathrm{~s}$ of all five integrators in unison. ( $T_{2}{ }^{\prime}$ and $T_{4}{ }^{\prime}$ follow automatically.) Methods for tuning an integrator were described in Part 8 (Figs 10 and 11). In particular, it was shown (Fig. 10(d) of Part 8) that by "plotting down" the input to an integrator by a factor $k(<1)$ the $T$ of the integrator is increased to $T / k$. When several inputs are summed at the virtual earth of an integrator amplifier it is obviously necessary to vary all these inputs. However, if thought is given to the placing of the potentiometers, each one may generally control an input to two integrators. This is achieved in Fig. 11 by breaking the circuit at the places marked X and feeding the potentiometers from the outputs of the adjacent amplifiers, the onward signal lines being reconnected to the sliders. It will be noticed that there also has to be a potentiometer in the input line; but the total number has been reduced to six, against the total of eleven separate inputs to the integrators.
The problem of providing a multi-gang potentiometer can be avoided by using the electronic switching method shown in Fig. 11 of Part 8. Using this method filters have been built covering a tuning range of 10 to 1 ; but because the action of "potting down" reduces the zero-frequency loop gain of the two-integrator loops (and hence their quality - see also Parts 5 and 7), some droop towards the corner of the pass-band response may be expected as the cut-off frequency is reduced, unless an adequate surplus of zero-frequency gain is provided.

## High-pass

In Part 7 it was shown how a two-integrator loop can be used to produce the basic 2nd-


Fig. 11. Realisation of a 5th-order Darlington low'pass response.


Fig. 12. High-pass sections.
order high-pass response. As a reminder of this, Fig. 12 shows an undamped high-pass section and the corresponding functional diagram. The essential feature is that the output, $V_{L}$, is obtained by subtracting the voltage across $C$ from the input $V_{i}$. This puts both integrators in the feedback path.

If the same principle is to be followed when a system of integrators is used to copy the working of a high-pass ladder structure, for example that shown in Fig. 13, it follows that the functional diagram must be arranged so that $V_{o}$ is derived from $V_{\text {in }}$ by successively subtracting voltages, $V_{6}, V_{4}$
and $V_{2}$, corresponding to those across the series-arm impedances of the passive circuit. As usual, it is convenient to work backwards from the output end, and so, assuming $V_{3}$ given, it is required to form the relationship

$$
\begin{equation*}
V_{0}=V_{1}=V_{3}-V_{2} . \tag{8}
\end{equation*}
$$

To do this, $V_{2}$ must be obtained by copying the working as follows:

$$
\begin{equation*}
I_{1} p L_{1}=V_{1} \tag{9}
\end{equation*}
$$

and hence

$$
\begin{equation*}
I_{1} R=V_{1} / p T_{1}\left(\text { where } T_{1}=L_{1} / R\right) \tag{10}
\end{equation*}
$$

$I_{2} R=I_{1} R+I_{0} R$ (where $I_{0} R=V$ ),

$$
\begin{equation*}
V_{2}=\frac{I_{2}}{p C_{2}}=\frac{I_{2} R}{p T_{2}} \text { (where } T_{2}=C_{2} R \text { ). } \tag{11}
\end{equation*}
$$

Similarly $V_{3}$ is obtained, assuming $V_{5}$ is given,

$$
\begin{equation*}
V_{3}=V_{5}-V_{4}, \tag{13}
\end{equation*}
$$

and so on.
The resulting functional diagram is deceptively simple. Turning it into a practical circuit using Blumlein feedback integrators and sign inverting stages leads to a formidable number of interconnections. At the output end, however, these may be reduced to more manageable proportions by using a modified integrator as shown in Fig. 14 which gives the voltage transfer ratio

$$
1+1 / p T_{1}
$$

In this way both $-V_{0}$ and $-V_{0} / p T_{1}$ are fed back together on a single wire (c.f. Fig. 7, Part 7).
It is also possible without much extra complexity to make additional connections to produce stop-band zeros, and quite highperformance filters have been built by this method. All things considered, however, other methods of building an active highpass filter, which will be described in a later article, are generally to be preferred.


| $T_{5}$ | $T_{4}$ | $T_{3}$ | $T_{2}$ | $T_{1}$ |
| :---: | :---: | :---: | :---: | :---: |
| $\frac{L_{5}}{R}$ | $C_{4} R$ | $\frac{L_{3}}{R}$ | $C_{2} R$ | $\frac{L_{1}}{R}$ |

Fig. 13. High-pass ladders.


Fig. 14. Electrical version of 5th-order h-p active ladder filter.

## Band-pass

The transformation of a low-pass ladder to band-pass was described in Part 2. Briefly, each reactance in the low-pass ladder is formed into a tuned branch by the addition, either in series for a series arm, or in parallel for a shunt arm, of a reactance of the opposite sort. Each of the tuned branches so formed is tuned to the same frequency, the geometric centre frequency of the required band-pass characteristic. Thus the shape and bandwidth of the band-pass characteristic are determined by the original low-pass filter, and the added reactances simply transfer the characteristic to the required position on the frequency scale. This process is illustrated in Fig. 15, where the output ends of passive ladders of alternative types, $\mathbf{T}$ and $\Pi$, are shown. The table shows the $T \mathrm{~s}$ which must be equal if the filters are to have the same bandwidth and (for the band-pass filters) centre frequency.
The working of these band-pass filters could be copied step by step, each reactance being considered individually; but the result can be reached more quickly by first noticing two related correspondences. The first, Fig. 16(a), is the familiar one (see Part 7, for example) between a two integrator loop and a series tuned circuit. When the parameters are appropriately matched, the active system in response to an input voltage $V$ produces an output voltage $I R$, which is proportional to the current $I$ which the same voltage produces in the passive circuit. The second, Fig. 16(b), is the correspondence between a two-integrator loop and a parallel tuned circuit. Here, when the parameters are appropriately matched, the active system produces an output voltage $V$ in response to an input voltage $I R$ which is proportional to the current $I$ which produces the same voltage $V$ across the passive parallel tuned circuit. In both cases $R$ may, in principle, have any arbitrary value.

Thus it is seen that an integrator representing an inductance is transformed to represent a series tuned circuit by connecting across it in a feedback link a second integrator, and that an integrator representing a capacitance is transformed to represent a parallel tuned circuit by the same addition. In each case the two-integrator loops so formed are tuned to the same frequency as the passive tuned circuit

It follows that the equivalent of the passive transformations shown in Fig. 17 is to connect a second integrator across each integrator of the active low-pass ladder to form a two-integrator loop. Each of these loops is tuned to the required centre frequency, and ideally gives infinite gain at this frequency just as the single integrators in a low-pass ladder ideally give infinite gain at zero frequency.




Fig. 15. Derivation of band-pass structures from low-pass.


Fig. 16. Active equivalents of the two types of tuned branch.

An example is shown in Fig. 17(b), where for convenience the arbitrary scaling resistance is taken as equal to the terminating resistance of the passive model, Fig. 17(a). The two-integrator loops representing the series-tuned branches develop $I_{1} R$ from $V_{1}$, $I_{3} R$ from $V_{3}$, etc.; and those representing the parallel-tuned branches develop $V_{2}$ from $I_{2} R$ etc. The interconnections via the several difference elements provide that (1) each two-integrator loop which represents a series-tuned branch is fed with the voltage across that branch, i.e. $V_{1}=V_{2}-V_{0}$, $V_{3}=V_{4}-V_{2}$, etc.; and that (2) each twointegrator loop which represents a paralleltuned branch is fed with a voltage proportional to the current through that branch, $I_{2} R=I_{3} R-I_{1} R$, etc.

For the sake of completeness Figs 17(c) and (d) illustrate the derivation of an active ladder from the alternative form of passive model; but since, for the same response, $T_{1}\left(=L_{1} / R\right)$ in the one form must equal $T_{1}\left(=C_{1} R\right)$ in the other, Figs 17(a) and (d), and so on for all the $T \mathrm{~s}$, the resulting active system, Fig. 17(d), is identical to that of Fig. 17(b).

The functional scheme derived above can be realised bya variety of means. If attention is confined to conventional feedback arrangements of the virtual-earth sort, it is necessary to take account of the sign reversal that accompanies each operation, and also to order the circuits so that subtractions are replaced by summations. A rule that must be followed is that all loops must
(a)


Fig. 17. Derivation of active band-pass ladder.


Fig. 18. Modelling the input end of a band-pass ladder filter.
contain an odd number of amplifiers, one or three. Each two-integrator loop must include a third amplifier for sign inversion, and a straightforward application of these rules gives Fig. 17(e). Clearly a large number of possible variations exist, though normally the circuits will be drawn to give a similar high degree of regularity. At the input end the action of the terminating resistance is easily reproduced as in Fig. 18, and again results in a resistor placed across the capacitor of an integrator.
When the filter modelled is of relatively narrow bandwidth the $T \mathrm{~s}$ of the integrators representing the reactances of the original low-pass filter, $T_{1}, T_{2}, T_{3}$ etc., are much larger than the $T \mathrm{~s}$ of the integrators representing the reactances added in the bandpass transformation, $T_{1}{ }^{\prime}, T_{2}{ }^{\prime}, T_{3}{ }^{\prime}$ etc. (because the low-pass corner frequency, which is also the band-pass width, is much smaller than the band-pass centre frequency). This, as we know from analysis of a single two-integrator loop, does not make good use of the integrator amplifiers. The flexibility of the active system is such, however, that a much larger resistance than $R$ may be chosen to give the two integrators in each loop approximately equal $T \mathrm{~s}$. This increases relatively the voltages at the outputs of the top row of integrators, and the resistances in all the remaining links connected to these points must be increased to compensate, if the bandwidth of the filter is to be unaltered.

## REFERENCES

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# Improving the 13A Oscilloscope 

# A few extra parts increase the bandwidth of this popular 'scope to $\mathbf{5 M H z}$ 

by N. W. Vale

The needs of scientific research and colour TV construction, both carried out on a limited budget, led the author to develop a modification which considerably improves the bandwidth of the Hartley 13A double-beam oscilloscope currently available at low cost on the surplus market. The instrument typically has a 3-dB bandwidth of 10 Hz to 3.5 MHz , although it will display a $4.5-\mathrm{MHz}$ signal of 3 V peak-to-peak.

The modified oscilloscope retains a maximum sensitivity of 300 mV peak-to-peak, and it has a virtually flat response from 20 Hz to 4.5 MHz . The $3-\mathrm{dB}$ points are at 10 Hz and 5 MHz .

Experiments with Wireless World colour TV circuits show that the modified oscilloscope will successfully display and lock video signals at the detector stage, giving a clear indication of the colour burst. It was found that all the important waveforms in the colour decoder could be readily displayed. In other tests the instrument was found to give a useful display at frequencies up to 10 MHz .

All extra components for the modification are easily fitted inside the oscilloscope case and the external appearance and control functions remain unaltered.

## General description

The bandwidth of the original instrument can be improved by reducing the value of the feedback resistor ( $R_{46}$ in the circuit diagram normally fixed inside the lid of each instrument) in the h.f. deflection amplifier.

Naturally, such a modification gives an appropriate loss of amplification. The deflection amplifier gain may be restored by adding a simple compensated wideband amplifier. A transistor design was originally considered for this application but was rejected for the wider dynamic range and better compatibility of a valve amplifier.

The compensated amplifier finally used is of conventional design and relies on the high slope of a frame grid r.f. pentode to obtain a good sensitivity while a low value of anode load is used to obtain the required bandwidth. Fig. 1 gives the circuit of this amplifier.

The 6 AK 5 is a triode-connected


Fig. 1. The circuit of the new wideband amplifier.
cathode-follower input stage, to obtain smooth gain control at high frequencies and maintain a high input impedance.

To provide compensation at high frequencies, the cathode resistor of $V_{2}$ is bypassed by $C_{4}$ the value of which has been selected to give compensation for the h.f. losses which occur in the oscilloscope and its active probe input circuits.

It is suggested that the modified oscilloscope be used with its cathode follower probe plugged in at all times. This is to avoid changes in the h.t. supply voltage to the new amplifier. In any case, it is advisable to use the probe for all work requiring the full frequency response of the modified instrument.

## Practical details

Remove the negative feedback resistor $R_{46}$ from the instrument and replace it with a $1.8 \mathrm{k} \Omega$ non-inductive carbon resistor rated at $0.5 \mathrm{~W}\left(R_{9}\right)$.

Interconnect contacts 1 and 2 of the probe switch $S_{4} A$ in the oscilloscope. This keeps the h.t. supply connected to the probe valve in all switch positions. The object of this is to prevent cathode poisoning of the probe valve, which might occur if the valve was allowed to run with heater only supplies for any length of time, and to keep the h.t. requirements for the input section as steady as possible.

Remove and discard $C_{35}$ (a large paper dielectric type). Fit two suitable valve holders in the region previously occupied by $C_{35}$ and build in the new amplifier. The
aluminium chassis bracket which passes the site of the new valves may have an appropriate piece cut out of it to allow easier access.

Remove the existing A1 gain control ( $R_{38}$ ) and connect the wire which originally fed this control from $R_{37}$ to the chassis. Fit $R V_{i}$, the new Al gain control, using the same panel hole.

Wire a $20-\mathrm{k} \Omega 10-\mathrm{W}$ resistor $\left(R_{10}\right)$ in parallel with resistors $R_{39}$ and $R_{40}$ of the oscilloscope. This compensates for the increased h.t. load due to the added valves.

Remove and discard $C_{34}$, the original input coupling capacitor to $V_{9}$, and connect new amplifier output to $V_{9}$.

Connect the input of the new amplifier to contact 6 on $S_{4} B$ (i.e. to A1 input) and check that the other connections to the new a mplifier are as shown in Fig. 1.

## Shopping list

| $R_{1}$ | $100 \Omega$ | $R_{7}$ | $2 \mathrm{k} \Omega^{*}$ | $C_{3}$ | $0.22 \mu \mathrm{~F}$ |
| :--- | :--- | :--- | :--- | :--- | :--- |
| $R_{2}$ | $2.2 \mathrm{M} \Omega$ | $R_{8}$ | $150 \Omega$ | $C_{4}$ | $820 \mathrm{pF} \#$ |
| $R_{3}$ | $820 \Omega$ | $R_{9}$ | $1.8 \mathrm{k} \Omega \dagger$ | $C_{5}$ | $16 \mu \mathrm{~F} b$ |
| $R_{4}$ | $10 \mathrm{k} \Omega *$ | $R_{10}$ | $20 \mathrm{k} \Omega \S$ | $V R_{1}$ | $5 \mathrm{k} \Omega$ lin. |
| $R_{5}$ | $100 \Omega$ | $C_{1}$ | $0.22 \mu \mathrm{~F}$ | $V_{1}$ | 6 AK 5 |
| $R_{6}$ | $100 \Omega$ | $C_{2}$ | $0.22 \mu \mathrm{~F}$ | $V_{2}$ | EF 184 |

$* 1 \mathrm{~W}$ rating. $\dagger 0.5 \mathrm{~W}$ rating. § 10 W rating.
All other resistors rated at 0.25 W . \#mica. b350V working.
All capacitors 250 V working polyester unless otherwise specified.

## Electronic Building Bricks

## 4. Transducers-analogue and digital

by James Franklin

In Part 2 we saw how information could be represented by electrical variables, both in static and dynamic form. A "travelling representation" is called a signal. Two examples given were pulses of electrical energy representing number of objects travelling on a conveyer, and a continuous variation of electrical energy representing sound-wave energy. To obtain these electrical signals a converting device was needed in each case-a photo-electric cell to convert the light energy and a microphone to convert the sound energy. There are in fact a great many converting devices in use, particularly in industrial control equipment. A familiar one at home is the gramophone pickup. Some convert the mechanical or other energy directly into electrical energy, as shown in Fig.1(a), while others-for example, the oven thermostat--use it to control electrical energy coming from a separate source, as shown at (b).

In Part 3 we saw that electrical energy is constituted by electrons, and that a general movement of many electrons is an electric current, measurable as a flow rate in coulombs per second (amperes). Current is an electrical variable, and as



Fig.1. Obtaining information in electrical form from information represented by some other type of energy: (a) direct energy conversion; (b) control of electrical energy.
such can be controlled. Thus in Fig.1(b) we could replace the words "electrical energy" by "electric current" or indeed by words denoting any other electrical variable. Also in (b) we could replace the words "mechanical (or other) energy" by
words describing a particular physical variable, such as force or temperature.

We can, in fact, develop from Fig. 1 a much more general concept-a device that receives some physical variable representing information and transforms this into an electrical variable representing the same information. The variables change but the essential information does not. Any actual device which does this is called a transducer*. This is our first "building brick", and we are showing it, according to plan, just as a functional block-Fig.2.



Fig. 2. Electronic building brick
No.1-the transducer; (a) an input
transducer; (b) an output transducer.
It must be quickly added that "transducer" can also mean a device that works in the reverse direction, converting an electrical variable into a physical variable, as shown at (b) in Fig.2. This may be thought confusing, but in practice the transducer's direction of operation in an electronic system becomes obvious from the position the device occupies in a block diagram, say at the input as against the output. Domestic examples of the Fig. 1(b) type of transducer are the loudspeaker and the television picture tube, though these are not often described as transducers. But the term is used frequently in industrial electronics (Fig. 2 (a) could be a "pressure transducer") and sometimes in sound reproduction.

From Part 2 we saw that information may be represented in a signal in two ways. In the electronic counting system the number of objects was represented by that number of pulses of electrical energy. In fact the exact form of the energy-time

[^1]


Fig. 3. Graphs illustrating the action of (a) an analogue transducer and (b) a digital transducer, both responding to angular displacement of a shaft.
graph did not matter very much: the pulses could equally well be triangular or some other shape provided their number was correct. This type of representation, in which the number of electrical events gives the essential information, is called a digital $\dagger$ signal.

With the other type of representation, the continuously varying electrical energy obtained from a microphone responding to a violin note, the successive values of electrical energy were proportional to the successive values of sound energy -they had to be, otherwise distortion of the information would occur. In other words the electrical energy timegraph was similar in form to the variation with time of the sound energy (supposing this were plotted as a graph). As such the electrical variable was a sort of model, or analogue, of the sound variable. Such a representation is called an analogue $\ddagger$ signal.

Some transducers are designed to work with analogue signals, others with digital signals-it depends on what is needed for a particular electronic system. For example, for a system in which a digital computer is the main element, digital transducers might well be the more convenient. To illustrate the difference between the modes of operation, Fig. 3 shows the relationships in two transducers, both representing a given physical variable, rotation of a shaft: (a) an analogue transducer giving a proportional electric current ( 3 milliamperes per degree of rotation), and (b) a digital transducer giving a related number of pulses of current (one pulse per 10 degrees). Both transducers use current as the electrical variable, the analogue type directly, the digital type merely as a medium for denoting number.

[^2]
## Circuit Ideas

## Hybrid push-pull deflection amplifier

A requirement arose for a push-pull deflection amplifier for an electrostatic cathode ray tube system where it was not practicable to provide the additional negative h.t. and heater supplies which would be required by the usual constantcurrent pentode coupling circuit. To satisfy the requirement a hybrid circuit was devised which uses a double triode valve in a standard long tailed pair configuration and a two terminal constant current circuit using transistors ${ }^{1.2}$ in the common cathode lead. Assignment of component values is very simple. First anode resistors and anode currents are chosen to meet the output requirements and this fixes the standing grid-to-cathode bias and the necessary input voltage swing. It is then possible to determine the offset voltage for the grids relative to ground from the inequality:- $V_{g g}+V_{g k}($ min $) \geqslant V{ }_{\text {cc (min) }}$ where $V_{g g}$ is the required offset voltage
$V_{g k}^{g g}$ is the grid-to-cathode voltage
$\left.V_{c \in}^{g k}{ }_{(m i n}\right)$ is the minimum voltage which can appear across the constant current circuit for correct operation
provided that a value for $V_{c c(\min )}$ is fixed. $V_{\text {cc }(\text { min })}$ is determined by the zener diodes,
the use of those with the lowest available reference voltage setting a lower limit for $V_{c c(m i n)}$ of about 7 V . If a smallest value for $\left.V_{g k(\min )}^{c c(m i n}\right)$ of 2 V is assumed, a minimum value of 5 V is established for $V_{g g}$ Use may be made of this offset voltage to provide a trace shift or picture centring facility as shown in the circuit diagram. The components shown provide a 460 V peak-topeak output swing for a 28 V peak-topeak input swing.
D. E. VAUGHAN, Christchurch, Hants.

1. P. Williams, "Letters to the Editor", Wireless World, p.456, Sept. 1966.
2. P. Williams, "Ring-of-two Reference", Wireless World, p.318, July 1967.

## Conversion of a double-beam scope for XY plotting

For those unable to buy an oscilloscope having identical X and Y amplifiers, the ability to do XY plotting is somewhat limited. The figure given illustrates a simple modification to a double-beam oscilloscope. The idle Y amplifier is made use of, and switched to the X plates,


Switching for X Y plotter.
which in turn have merely been disconnected from their own amplifier. Leaving the spare beam disconnected at the upper Y plates usually means that it will appear near centre on the screen, but with the brilliance turned down, no difficulty should ensue. Where the output of the normal X and Y amplifiers is developed with respect to chassis, care should be taken to avoid reversals in the switching.
B. LANE,

Bletchley,
Bucks.

## Connecting microphones to transformers

It is sometimes necessary to be able to connect either a balanced or unpalanced input plug to the primary of a microphone transformer. This can be done with the circuit shown which allows either to be plugged into its appropriate socket. The


Versatile microphone transformer arrangement.
jack sockets have normally closed contacts as shown, and the connections are arranged so that the whole of the primary winding is included and the appropriate points and cable screening are earthed in each case. A floating balanced input can also be obtained by inserting an empty plug into the unbalanced socket.
A. C. Gott,

Southall,
Middx.

# The F.E.T. as a Class-A Audio Amplifier 

## When to use and how to bias

by P. L. Matthews*

In spite of the publicity given to field-effect transistors when they were introduced, they are still dominated by bipolar types in audio circuits. One of the main reasons for this is that present methods of manufacture lead to wide variations in their primary charac-teristics-the zero gate voltage drain current $I_{d s s}$, pinch-off voltage $V_{p}$, and mutual conductance ${ }_{g m 0}$-which are approximately related by $2 I_{d s s}=g_{m 0} \cdot V_{p}$.

Probably the most widely used f.e.t. is the 2 N 3819 , with $V_{p}$ and $I_{d s s}$ spreads of 0.5 to 7.5 V and 2 to 20 mA respectively. Without going into calculations it can be seen that if devices with extreme parameter values are to be incorporated into a conventional selfbiased stage, the design will have to tolerate a drain current variation of the order of 10 to 1 , which is obviously impracticable. The extra cost of a tightly specified selection of the 2N3819 makes it less of an economic proposition when a couple of cheap plastic bipolars will often do the job just as well. However, there are some instances in which an f.e.t. must be used, and this article aims to show which devices should be chosen for a given application, and how they should be biased.

## The perfect performance

In order to determine how bias variations alter the performance of an f.e.t. amplifier it is useful to consider the operation of a theoretically perfect device in an isolated self-biased stage. The circuit of Fig. 1 depicts an n -channel f.e.t. operated from a supply voltage of $+V_{d d}$, with load and bias resistors $R_{L}$ and $R_{S}$ respectively, when capacitor $C$ is sufficiently large to bypass signal frequencies. The input shunting resistor $R_{g}$, which
*Newmarket Transistors Ltd.


Fig. I. Standard biasing circuit for f.e.t. audio stage.


Fig. 2. Values of $c$ for various values of a and $b$, according to the equation.
would typically be about $1 \mathrm{M} \Omega$, must nevertheless be small enough to ensure that $R_{g} \cdot I_{g s s} \leqslant V_{g s}$ and the gate terminal can then be considered to be at zero d.c. potential. In addition the primary characteristics of the f.e.t. are taken as $V_{p}, I_{d s s}$ and $g_{m}$.

From the above it can be seen that, provided the input signal remains within the linear region, the maximum $\mathrm{pk}-\mathrm{pk}$ output voltage swing in the linear region ( $V_{d s}>V_{p}$ ) is

$$
\begin{aligned}
& V_{d d}-\left[V_{d s(s a t)}+V_{g s}\right] \\
= & V_{d d}-\left[\left(V_{p}-V_{g s}\right)+V_{g s}\right] \\
= & V_{d d}-V_{p} .
\end{aligned}
$$

The voltage drop across $R_{L}$ is half the swing, or $\frac{V_{d d}-V_{p}}{2}$, and this gives the optimum value of $R_{L}$ as

$$
R_{L}=\frac{V_{d d}-V_{p}}{2 I_{d}}
$$

But $A_{V}=g_{m} \times R_{L}$
$=\frac{2 I_{d s s}}{V_{p}}\left(1-\frac{V_{g s}}{V_{p}}\right) \times \frac{V_{d d}-V_{p}}{2 I_{d}}$
$=\frac{V_{d d}-V_{p}}{V_{p}-V_{g s}}$ (with substitution for $I_{d}$ ).
Again, considering $\mathrm{pk}-\mathrm{pk}$ signal voltage,

$$
V_{\text {in(max })}=\frac{V_{\text {out }(\max )}}{A_{V}}
$$

This gives $V_{i n(\text { max })}=V_{p}-V_{g s}$.
This result shows that no matter what other specifications the f.e.t. has, provided that the load resistance is substantially lower than the input impedance of the following stage, and that the drain voltage falls exactly at the centre of the output swing, an input signal of $V_{p}-V_{g s}(\mathrm{pk}-\mathrm{pk})$ gives the maximum output of $V_{d d}-V_{p}$ ( $\mathrm{pk}-\mathrm{pk}$ ). Consequently, a device with a low pinch-off voltage should be selected for use with a low supply voltage so that a larger output swing will be available. As a general rule, it is not worthwhile operating an f.e.t. from a supply voltage less than twice its maximum pinch-off voltage, so the 2 N 3819 would have to run off at least 15 V . You have to be careful, of course, not to exceed the maximum voltage rating for the device -in this case it is 18 V .
It is now easy to calculate the harmonic distortion (predominantly second) produced by the above amplifier at maximum output.

$$
D_{2}=\frac{V_{i n}}{8\left(V_{p}-V_{g s}\right)}=\frac{1}{8}=12 \frac{1}{2} \% .
$$

It may seem remarkable that the above simple results should hold for any depletion mode f.e.t. but in practice a slight departure from the theoretical value would be expected due to variations in the specification of $V_{p}$, and to the fact that the assumed equations may only be approximately true.

## The problem of parameter spreads

The selection of suitable bias conditions for the f.e.t. is now considered. With a particular device, it can be seen that as $V_{g s}$ is increased toward $V_{p}$, more voltage gain is obtained at the expense of output swing, and vice versa. A higher supply voltage increases both gain and output, but, as the designer is often tied to the supply of 12 V or so available in most equipment and because the drain-source breakdown voltage (which is only about 20 V for many popular devices) imposes limitations, this is not always a practicable proposition. Nevertheless, a quick calculation will show that quite a reasonable gain and output can be obtained with a typical f.e.t. but the problem of parameter spreads now becomes clear. If a circuit is set up with components selected to suit a device with a chosen $V_{p}$ and $I_{d s s}$ substitution of a dissimilar device is
likely to cause severe bias problems. In particular, the variation in drain current will upset the vital centring of the drain voltage between $V_{d d}$ and $V_{p}$, causing a considerable reduction in output voltage swing. Unfortunately this problem cannot be solved in general as simply as in the preceding calculations, and the best technique is to determine the maximum spreads of $I_{d s s}$ specified for the device in question, and then to calculate the optimum resistance values for a typical centre spread unit. As an example, in the case of the 2 N 3819 , it would be best to take $I_{d s s}=11 \mathrm{~mA}$ and $V_{p}=4 \mathrm{~V}$, as these are the middle values. It also proves useful to specify $V_{g s}=\frac{V_{p}}{2}$ in most cases, as this places the input voltage swing safely in the centre of the permitted region.
Suppose, in the circuit of Fig. 1 that a device with parameters $I_{\text {dss }}$ and $V_{p}$ are inserted, $R_{S}$ is adjusted to make $V_{g s}=\frac{V_{p}}{2}$, and $R_{L}$ sets the drain voltage to the middle of the output swing. The drain current is therefore $\frac{I_{\text {dss }}}{4}$. If now the f.e.t. is removed and replaced by a device with parameters $I_{\text {dss }}$ and $V_{p^{\prime}}$, where $I_{d s s^{\prime}}=\left(a . I_{d s s}\right)$ and $V_{p^{\prime}}=$ ( $b . V_{p}$ ) ( $a$ and $b$ are small positive numbers) then the new drain current $I_{d^{\prime}}$ can be related to the original by $I_{d^{\prime}}=c . I_{d^{d}}$.

Substituting into the standard transfer equation,

$$
I_{d^{\prime}}=I_{d s s^{\prime}}\left(\frac{V_{p^{\prime}}-V_{g s^{\prime}}}{V_{p^{\prime}}}\right)^{2}
$$

giving

$$
c I_{d}=a I_{d s s}\left(1-\frac{c}{2 b}\right)^{2}
$$

and thus

$$
c^{2}\left(\frac{a}{b^{2}}\right)-c\left(\frac{4 a}{b}+1\right)+4 a=0
$$

The solution of this quadratic is

$$
c=\frac{b^{2}}{2 a}\left(\frac{4 a+b}{b}-\frac{\sqrt{8 a+b}}{b}\right)
$$

and further simplification gives

$$
c=\frac{b}{2 a}[(4 a+b)-\sqrt{b(8 a+b)}]
$$



Fig. 3. Graph showing proportionality between $V_{p}$ and $I_{\text {dss }}$ for NKT80110 familytypical for most popular devices.

Approximate values of $c$ for various values of $a$ and $b$ are given in Fig. 2.

This discussion assumes to a certain extent that the highest and lowest values of $V_{p}$ and $I_{d s s}$ occur simultaneously, so that they are considered to be characteristic of an extreme device. In theory this is not necessarily the case, but the graph in Fig. 3 illustrates that $V_{p}$ can be considered to be roughly proportional to $I_{\text {dss }}$ for devices from the Newmarket NKT801 10 family, and this can be shown empirically for most popular devices. In any event it is possible to allow for discrepancies of this nature merely by substitution of appropriate "worst cases" in the above equation.

## A practical example

An example will help to clarify the general procedure. Consider the circuit shown in Fig. 4(a) which incorporates a junction f.e.t. type NKT80212. The typical $V_{p}$ and $I_{\text {dss }}$ for this device are 700 mV and $200 \mu \mathrm{~A}$ respectively, and setting $V_{g s}=\frac{V_{p}}{2}=350 \mathrm{mV}$ gives a drain current of $50 \mu \mathrm{~A}$. The values of $R_{S}$ and $R_{L}$ can be calculated from this information to be $7 \mathrm{k} \Omega$ and $83 \mathrm{k} \Omega$ respectively and the nearest E12 preferred types have been specified in the diagram.

Consider now what happens when this typical device is replaced by a "lower spread" unit with $V_{p}$ and $I_{d s s}$ of 500 mV and $100 \mu \mathrm{~A}$ respectively as shown in Fig. 4(b). For this unit, $a=\frac{1}{2}, b=\frac{5}{7}$ and this gives $c=0.6$ (approximately) so the new drain current will be about $30 \mu \mathrm{~A}$. The source and drain voltage can now easily be calculated and it is seen that the drain voltage is above the output swing centre, causing clipping of the waveform unless its amplitude is reduced to 2.5 V pk-pk. A similar argument applies to the "upper spread" unit with $a=1 \frac{1}{2}$, $b=1 \frac{2}{7}$ and $c=1.35$ (approximately), giving $I^{\prime}=68 \mu \mathrm{~A}$, but this time the drain voltage is too low and restricts the output to 2.5 V $\mathrm{pk}-\mathrm{pk}$. Thus the circuit will be able to yield an output of only $2.5 \mathrm{~V} \mathrm{pk}-\mathrm{pk}$ at most for any NKT80212 f.e.t. without individual circuit adjustment, as distinct from just over $8 \mathrm{~V} \mathrm{pk}-\mathrm{pk}$ for the typical device considered first.

The distortion level appears to be rather complicated to calculate, but it is sufficiently accurate to consider the ratio of available output to maximum output and multiply this by the previously determined value of $12 \frac{1}{2} \%$. In this case the value would be $D_{2}=\frac{2 \cdot 5}{8} \times 12 \frac{1}{2} \%=4 \% \quad$ (approximately). The justification for this calculation is understandable in the case of the typical device, as $D_{2}$ is proportional to $V_{i n}$, but this can be formally extended to cover the limit cases if desired.

## The effect of temperature

Variations in temperature, supply voltage, resistor values, etc., can readily be incorporated into the above argument, but, as the first of these can be very important, a brief outline of the method is given. The pinch-off voltage of an f.e.t. decreases with

(a)

(b)

(c)

Fig. 4. Circuits illustrating the effect of parameter spreads in f.e.ts.
temperature by a factor similar to that of a p-n junction, a typical value for diffused devices being $-2 \mathrm{mV} / \mathrm{C}^{\circ}$. Unfortunately it is not as easy to define a simple factor for $I_{d s s}$ as this depends on such things as carrier mobility and impurity concentrations of the particular device, but many manufacturers provide a graph of the relationship. As a guide, however, it can be estimated that $I_{\text {dss }}$ will fall linearly with increase in temperature up to $75^{\circ} \mathrm{C}$, when its value is $\frac{3}{4}$ of that at $25^{\circ} \mathrm{C}$. Conversely, the $I_{\text {dss }}$ at $-25^{\circ} \mathrm{C}$ is $1 \frac{1}{4}$ times the value at $25^{\circ} \mathrm{C}$. If the previously designed amplifier was required to operate from $-25^{\circ}$ to $+75^{\circ} \mathrm{C}$ it would be necessary to consider the typical device at $25^{\circ} \mathrm{C}$ as before, the lower spread device at $+75^{\circ} \mathrm{C}$ and the upper at $-25^{\circ} \mathrm{C}$. These would give a $V_{p^{\prime}}$ and $I_{d s s^{\prime}}$ of 400 mV , $75 \mu \mathrm{~A}$ and $1 \mathrm{~V}, 375 \mu \mathrm{~A}$ for them, respectively, so $a, b$, and subsequently $c$ would be altered accordingly.

## Conclusion

"You pays your money, you takes your choice". Either you select an economical "full spread" device and accept its restricted usefulness, or pay more for a special selection with its corresponding advantages. It's not surprising that bipolar transistors are still the first choice for most audio circuits.

## Personalities

Paul Adorian, F.C.G.I.. F.I.E.E. F.I.E.R.E., managing director of Rediffusion Ltd since 1966, is to retire at the end of October when he will be succeeded by Hugh Dundas, D.S.O.. D.F.C., D.L. who has been on the board of the company since 1966. Mr. Adorian. who will be 65 in November. entered the field of radio communications as a student engineer with Standard Telephones and Cables. He joined Rediffusion in 1932 as a development engineer, becoming in succession assistant chief engineer and chief engineer before joining the board. He is also chairman of Redifon Ltd, manufacturers of flight simulators and communications equipment, and of Redifon-Astrodata Ltd and a director of the British Electric Traction Company Ltd. Mr. Dundas. his successor, joined Rediffusion's executive staff in 1961 from the Beaverbrook Press. He is also a director of Rediffusion's parent company, British Electric Traction, and of Thames Television.

Sinclair Radionics has bought a major shareholding in the AIM Associates Group. Tim Eiloart, founder of the group, has resigned from the position of chief executive but remains outside chairman of Cambridge Consultants Ltd, the research and development company of the AIM group, and Richard Cutting is appointed managing director. Gordon Edge and Roy Hawkins, who were joint managing directors of Cambridge Consultants, have left the company and been appointed to the Technical Division of PA Management Consultants Ltd. David Southward, another of the founder-directors of the company, remains managing director of AIM Electronics, AIM bioSciences and Cambridge Audio Laboratories, the Group's manufacturing subsidiaries. Clive Sinclair, manag ing director of Sinclair Radionics, which he founded eight years ago, has become chairman and chief executive of the AIM group. Mr. Sinclair has stated that the two organizations will operate independently "because of their very different fields of activity".

Commander David W. Malim has become chairman of Marconi Space and Defence Systems Ltd, one of the four systems companies within GEC-Marconi Electronics Ltd. Educated at the Royal Naval College, Keyham, he served as an officer in the Royal Navy throughout the war and was on the staff of the British Joint Services Mission in Washington from 1946 to 1949 when he went to the Admiralty as weapon engineer officer. On his retirement in 1959 Commander Malim became manager and director of Lancashire Dynamo Ltd, in Manchester, joining Elliott Automation Ltd in 1962 and becoming joint managing director of Elliott Space and Weapon Automation Ltd in 1963. English Electric bought Elliott Automation in 1968 and after the merger with GEC in 1969 all the electronics interests in the group were reorganized. Elliout Space and Weapon Automation became part of GEC-Marconi Electronics Ltd and Commander Malim was appointed joint managing director of GEC-Elliott Space and Weapon Systems with Arthur S. Walsh, M.A. (Cantab.), who now becomes managing director of Marconi Space and Defence Systems. Mr. Walsh, who is 44, was educated at Selwyn College, Cambridge, where, after service in the Royal Signals from 1944 to 1948, he graduated in natural sciences in 1951. He joined the GEC Laboratories at Stanmore in the radar microwave group and became a group leader in 1956. Mr. Walsh was appointed assistant manager of the Applied Electronics Laboratories at Stanmore in 1964, becoming manager a year later, and was technical director of GEC-AEI (Electronics) Ltd from 1966 until his appointment as joint managing director of GEC-Elliott Space and Weapon Systems Lid in 1969.

Leo G. Dive, the senior assistant in the B.B.C. Engineering Information Department, is to be the Corporation's engineering representative on the B.R.E.M.A. commercial committee in succession to Hugh Greatorex, who
retired recently. Mr. Dive, who was from 1964-1966 senior engineer in the B.B.C's New York Office, has also taken over responsibility for the management and direction of the B.B.C's mobile colour demonstration unit which is at present on a summer tour of exhibitions and promotions. Enquiries about the unit should be addressed to Mr. Dive at the Engineering Information Department, B.B.C.. Broadcasting House. London WIA IAA.

Eric J. Wightman has been appointed engineering director of the Industrial Instrument Division of Smiths Industries Ltd. Mr. Wightman, who is 43 , has spent a little over three years with the Industrial Instrument Division, first as chief engineer and latterly as technical manager. Before joining S.I. he spent two years as chief engineer, data systems, at Solartron and previously was with the Gyroscope Division of Sperry Rand for seven years.
K. Milne, Ph.D., M.I.E.E., has been appointed engineering manager of the Radar Equipment Division of Plessey Radar Ltd in succession to R. L. Burr, who has become technical co-ordinator for Plessey Radar. Dr. Milne began his career in 1946 as chief microwave aerial designer with Associated Electrical Industries Ltd. He was awarded his doctorate in 1951 for his thesis on wide-angle scanning properties of microwave lens aerials. In 1953 he became engineeer-in-charge of systems analyses of radar systems, including c.w. and volumetric scanning radar. He joined Decca Radar Ltd in 1960. Particular projects with which he was concerned included satellite earth terminals and electronic scanning radars. He was appointed manager of Plessey Radar's Space Systems Department in 1966.
J. W. V. Denton is appointed national sales manager by Data Recognition Ltd, of Reading. Prior to joining D.R. he was manager, information systems, for Motorola Control Systems Ltd and before that was with Cossor Communications for four years as their regional sales manager. Mr Denton received his training in communications and radar in the Royal Navy.

Sir Robert Cockburn, K.B.E., C.B., has been appointed chairman of the Council of the National Computing Centre. He succeeds J. M. A.Smith, who recently retired. Sir Robert, who is 61 , was director of the Royal Aircraft Establishment, Farnborough, from 19641969. A graduate of London University, he engaged in research in communications, radar and atomic energy between 1937 and 1948 at R.A.E., the Telecommunications Research Establishment and the Atomic Energy Research

Establishment, respectively. He was the Scientific Adviser to the Air Ministry from 1948 to 1953 and between 1954 and 1959 was successively principal director of scientific research (guided weapons and electronics), deputy controller of electronics, and controller of guided weapons and electronics at the Ministry of Supply. Sir Robert, who received his knighthood in 1960, was chief scientist. Ministry of Aviation, from 1959 to 1964, and vice-chairman of the Space Committee, Ministry of Defence. from 1964-1965.

Transitron Electronic Corporation. of Wakefield, Mass., has announced the appointment of Grahame F. Hazell as vicepresident for European Semiconductor Operations. Mr. Hazell, who is 36 , is a native of Ipswich, Suffolk, and a graduate in physics of the University of Nottingham. For the past 10 years he has been employed by Texas Instruments, initially on various marketing assignments and for the past few years as operations manager of the TI facilities in Bedford and, more recently, Plymouth. The Transitron companies reporting to European Semiconductor Operations are in the UK, France, West Germany, Holland and Sweden.

George Siddall, who joined the Electrical Research Association as head of its Electronics Department in 1962, has been appointed assistant director technical to help Dr. B. C. Lindley, the director, in the formulation, co-ordination and control of the Association's technical policies and operational activities. He will have special responsibility for the Applied Sciences Division and for the technological planning unit.

Robert W. Beattie has resigned from the managing directorship of Electrosil Ltd and chairmanship of Miniature Electronic Components Ltd. He is succeeded in these positions by John E. Carl, B.Sc., a 42-year-old American who recently came to this country from the parent company Corning Glass Works. After graduating from Alfred University, New York, in 1951 with a degree in ceramic engineering he joined the research and development department of Corning. In 1968 he moved to the electronic components plant at Bradford, Pennsylvania, where he remained as plant manager until coming to the U.K. recently as production executive at Pallion, Sunderland.

## OBITUARY

John Goodman, assistant managing director of the Dubilier Condenser Co. (1925) Lid, died recently at the age of 56 . Mr. Goodman joined the company in 1932, and was appointed assistant managing director in 1966. His father was one of the founders of the company in 1912.

## World of Amateur Radio

## Awards and certificates

Although amateur operating proficiency awards and certificates have a long and respected history--for example, the "worked all continents" award dates back to the early days of the International Amateur Radio Union, founded in 1925-there are fears that the situation has rather got out of hand in recent years. As far as can be judged there are now between 800 and 1000 different awards issued by national and international societies and groups, local clubs, and in association with various amateur radio publications. While many of these do undoubtedly encourage useful activities and provide amateurs with valuable competitive yardsticks, there is a growing belief that unless care is exercised the rising flood of awards may bring the system into disrepute. The recent introduction of new awards, such as the "five-band DXCC" requiring some 500 QSL cards, valid only if of recent date, is threatening to overwhelm the amateurs in the "rarer" countries with requests for more and more cards. For several years some of these amateurs have appointed "QSL managers" to undertake the tremendous task of verifying thousands of brief radio contacts each year. But even so (and there are arguments against the system of QSL managers as this is open to abuse), it is becoming more and more difficult to obtain the rarer cards from overseas stations swamped by requests.

The R.S.G.B.-which has done much to uphold the continued value of proficiency awards--has recently announced new rules for all of its awards (details from R.S.G.B., 35 Doughty Street, London W.C.1), but one notes with some alarm that yet another major new award "The I.A.R.U. Region I Award" has been added to the list-this time at the request of the I.A.R.U. Region I Bureau.

## R.A.E. courses

Would-be amateur transmitters should note that a number of evening courses covering the syllabus of the Radio Amateurs Examination will be starting at local educational centres in many parts of the country during September. Typical of these is one at Birkenhead Technical

College where enrolment takes place from September 7 to 10, and classes are held on Thursday evenings. In this area, as in a number of others, Morse classes are held in conjunction with the local amateur radio society, in this case the Wirral A.R.S. (non-members enquiries to Alf Fisher, G3WSD, 34 Glenmore Road, Oxton, Birkenhead. We have been notified of courses at several London centres including Acton Technical College. Wembley Evening Institute and Gascoigne Recreation Centre, Barking. Readers in other parts of the country should make inquiries of their local education authority to discover if there are any local courses.

## Transceivers

Although Collins introduced an h.f. transceiver about 10 years ago, it is only quite recently that fairly substantial numbers of amateurs have swung over to the use of compact, combined transmitter-receivers.

While transceivers are generally regarded as fairly ambitious projects for home construction, many of the problems can be overcome by group construction. For example, the Nottingham Amateur Radio Club is planning a constructional project this winter under the guidance of Bob Sills, G31QM, for a number of members to build their own five-band, largely solid-state, s.s.b. transceivers at a cost in the region of $£ 30$.

An interesting recent development in the field is the marketing in the United States of a compact 2 -watt c.w.-only low-power transceiver for 3.5 and 7 MHz , for use as a fixed or vacation station. The key feature of this all-semiconductor equip ment, which runs from dry batteries and is made by Ten Tec for sale at about $\$ 55(£ 23)$, is the use of its single variable-frequency oscillator to form the transmitter driver and a simple homodyne (synchrodyne) receiver based on, a dual-gate m.o.s.f.e.t. heterodyne detector, and with a single integrated circuit providing all the a.f. amplification.

At the other end of the scale is the recent 300 -watt p.e.p. CX7 transceiver by Signal /One, a subsidiary of the computer firm N.C.R. This makes full use of s.i.cs, including 16 digital and 14 linear types, 60
silicon transistors (including dual-gate f.e.ts in the front-end) with one ceramic/metal power valve which has a beryllia coupler block to transfer anode heat to its own extruded heat sink and with many other features to put it into the de luxe class.
In Brief: Winner of the 1970 (33rd) annual B.E.R.U. Contest was R. J. Mills, VQ8CR, of Mauritius, who made 517 contacts in spite of very poor propagation conditions. Runner-up was D. M. MacVicar, VP7DX, while D. L. Courtier-Dutton, G3FPQ, was third and the leading British station. ... A new v.h.f. beacon transmitter, GB3DM, is now operating from the I.T.A. transmitting site at Burnhope, Co. Durham. The 30 -watt tiansmitter on 145.975 MHz feeds two four-element Yagi aerials beaming north and south, mounted at a height of 98 ft . The station can be received at good range (reports to D. Long, G3PTU, Croesor, Iveston Lane, Iveston, Leadgate, Consett, Co. Durham). . . . Among recent stations heard on h.f. bands have been FB8XX (Kergulen Islands), 4N2BR (a Yugoslav expedition to one of the Adriatic Islands), HS5ABD Chaing Mai, Thailand, 9 Q5QR Kinshasha, Congo, and the Japanese EXPO ${ }^{\prime} 70$ station JA3XPO. Also reported active recently have been CEOAE Easter Island, VPICP British Honduras, VR5LT Tonga Island and several CE9A stations on South Shetland Island. . . . An intense E-layer disturbance on July 6th resulted in long-range reception of many v.h.f. broadcasting stations on 70 and 95 MHz , and another opening to TF3EA in Iceland. . . . Among the mobile rallies being held in September are: R.S.G.B. Scottish Mobile Rally (19th) at the David Livingstone Memorial, Blantyre, Lanarkshire (details G. A. Hunter, GM3ULP, "The Bungalow". Broomside Braes, Camp Road, Motherwell); Peterborough (20th) at Walton Senior School, Mountsteven Avenue off Lincoln Road, Peterborough; and Harlow (27th) at Magdalen Laver Village Hall (details B. ' G. Capper, G8CUA, 124 Peterswood, Harlow, Essex). ... A special event station, GB3WAC, will be operating from the Sea Cadet's HQ, Scotch Yard, Tonypandy, during the World Archery Championships (Sept. 10th-12th). . . A special station, GB3CWR (or GB3CWI) will be run in connection with the Cumberland Federation of Women's Institutes "Golden Jubilee" celebrations (Sept. 6th-12th). . . . Contests during September include the V.H.F. National Field Day (6th) in conjunction with the international I.A.R.U. contest; "Worked all Europe" DX Contest (12th to 13th, phone section): $3.5-\mathrm{MHz}$ Field Day (13th); and National Final of the R.S.G.B. D/F contest (20th. by Slade Radio). . . . A new world record for 13 cm is being claimed for a 249 -mile contact in the United States (W4HHK and WA4HGN/P). . . . A $144-\mathrm{MHz}$ moon-bounce contact has beer made between New Zealand (ZL1AZR) and California (K6MYC).

PAT HAWKER, G3VA

## Literature Received

## For further information on any item include the $W W$ number on the reader reply card

## ACTIVE DEVICES

Power microcircuits are the subject of some literature we have received from AEI Semiconductors. Carholme Rd. Lincoln.

PM5A. Thyristor/rectifier diode combination, $800 \mathrm{~V}, 5 \mathrm{~A}$ $\qquad$ WW401
PM 6A. Diode/diode. 1.4kV. 6A .....WW402
PM 7A. Bridge rectifier. 1.4 kV . 7A ..WW403
Motorola have produced a new journal called Semiconductors which is to be produced every 3 months. The first issue contains articles on integrated circuits for industry and computers. gives circuits for a 400 MHz wideband amplifier. a 1 Hz low-pass filter. and low-voltage inverters. and describes an integrated circuit f.m. stereo decoder ...WW404

A 96-page manual called "Power transistors for amplification switching and control" has been produced by RCA. It covers physical theory. structure. packaging. limiting factors. and the operation and requirements of power transistors in amplification. switching and in control circuitry. The price is $\$ 2$. RCA Solid State Division. Somerville. N.J.08876. U.S.A.

A range of logic modules employing. high threshold logic. d.t.1.. t.t.l. and e.c.l. are the subject of a catalogue from Jasmin Electronics Ltd. 1 Meriden Close. Hainault. Ilford. Essex. The products consist of integrated circuits on printed circuit cards $\qquad$ WW405
"Reliability Report-digital integrated circuits -May 1970" may be obtained from the National Semiconductor Corporation, 2900 Semiconductor Drive. Santa Clara. California 95051
.WW406
"Planar Power Switching Transistors" is the title of a new Mullard publication for design engineers. E.E.D.. Mullard Ltd. Mullard House, Torrington Place. London WC1E 7HD .
.WW407
Marconi-Elliott Microelectronics Ltd. Witham. Essex. have recently started production of 54.74 series t.t.l. and have published a data sheet on their range

WW408

## PASSIVE COMPONENTS

Bulletin 94033 from Brush Clevite Co. Ltd. Thornhill, Southampton, Hants. describes a 10.7 MHz ceramic filter (type FM4) intended for use in f.m. i.f. strips. The component has a 3 dB bandwidth of typically 235 kHz ( 40 dB . 900 kHz max.) and an insertion loss of about 3.5 dB

WW409

An alarm annunciator capable of displaying. 12. 18 or 24 legends is described in a data sheet from Mimic Diagrams and Electronics Ltd. Maxim Rd. Crayford. Kent. The unit contains logic for alarm sequences ......WW4 10

Condensed catalogue 8010 from Penny and Giles Lid. Mudeford. Christchurch BH23 4AT. Hampshire. deals with a range of precision conductive plastic potentiometers ........WW41I From the same company comes a fuller catalogue containing details of rectilinear and rotary potentiometers: pressure. force. acceleration and rotary transducers: and servo and signal conditioning equipment .......WW412

A wall chart devoted to wirewound trimming potentiometers may be obtained from Electrosil Ltd. Pallion. Sunderland. Co. Durham

WW 413
"Manual of inverter transformers and modules" has been published by Gardners Transformers Ltd. Christchurch. Hampshire BH23 3PN .WW414

A pocket booklet describes the products of B \& R Relays Lid. Temple Fields. Harlow. Essex.

WW415
Limit switches. microswitches and proximity switches together with various process timers are the subject of a new 20 -page catalogue from Omron Precision Controls. 313 Edgware Rd. London. W.2. $\qquad$ WW416

We have received the following literature concerned with audio equipment for professional use from Vitavox Ltd. Westmoreland Rd. London. N.W.9.

B80 and B M 100 microphones ........WW417 B50 series microphones .......................WW418
B60 and B64 microphones ...................WW419
Microphone stands ............................WW420
Pressure units data sheet
Type 190 circular horn ...........................WW422

- Radial diffuser. lightweight hailer and

1000 Hz horn .....................................WW 423
Series 550 multicell horns .................WW424
Series 220 multicell horns .................WW425
Bitone loudspeaker systems (halls and cinemas) ............................................WW426
Mini-bitone speaker system (special effects
in halls and cinemas) ........................WW427
Dividing networks (cross-over) ........WW428 15 -inch ( 380 mm ) ceramic magnet loudspeakers WW429
12 -inch ( 305 mm ) ceramic magnet loudspeakers ............................................WW430
3-inch ( 84 mm ) WN 350 loudspeaker unit ......
WW431
Trade price list
WW432

An integrated circuit patchboard which will house up to 14 packages (or more with a plug-in extension board) and which contains pulse generation. input and indication facilities is described in a leaflet from Elliott Instruments Ltd. Station Industrial Estate. South Woodham Ferrers. Nr. Chelmsford. Essex ............WW433

## APPLICATION NOTES

A leaflet "Use of 10.7 MHz ceramic coupled mode filters in linear i.c. i.f. strips" is obtainable from the Brush Clevite Co. Ltd. Thorn hill. Southampton. Hants ...........WW434
"Power Microcircuit" describes the use of the PM5A. 6A and 7A devices mentioned in the Active Devices section. AEI Semiconductors. Carholme Rd. Lincoln WW435

Application report No. 6 from Brookdeal Electronics Ltd. Market St. Bracknell. Berkshire is called "Measurement of contact potential by the vibrating capacitor method" ....

WW436

## EQUIPMENT

High-quality audio power amplifiers for use in the broadcasting and sound recording industries with outputs up to 100 W are the subject of a leaflet from $H / H$ Electronic. Industrial Site. Cambridge Rd. Milton. Cambridge CB4 4AZ

WW437
The following catalogues of American equipment are available from Wessex Electronics Ltd. Stover Trading Estate. Yate. Bristol BS 17 5QP.

Wiltron Company. Sweep generators 0.1 to 18 GHz . phase meters. vector network analysers. line stretchers. v.s.w.r. automatic testers. directional detectors and r.f. detectors ...........................WW438
Anzac Electronics. Broadband r.f. and microwave signal processing devices. 0.5 M Hz to 3 GHz .
....................WW439
Wavetek Company. Function generators from sine. square and triangle manual instruments to fully programmable waveform synthesizers from 0.0015 Hz to 10 M Hz WW440
Philco-Ford. Sierra Operations. High-power signal generators 50 MHz to 3 GHz . watt meters. coaxial loads and attenuators ................................................WW441
Birtcher Corporation. Transistor and integrated circuit test equipment. computer controlled automatic test equipment .....................................WW442

The data sheets listed below were sent to us bv Beglec N.V.. 718 Houba de Strooperlaam. Brussels 2.

Rodec Fader. 22 Hz to 32 kHz .........WW 443
Rodec Stereo Mixer. CU887. Four-channels with bass and treble controls. comprehensive switching facilities and twin VU meters $\qquad$ ..WW444
Rodec Mixer. CU881. Four-channel stereo mixer ..WW445

Audio equipment. an amplifier (model 9000) and an f.m. tuner (model 1500). is described in literature from Bryans Amplifiers Ltd. 18 Greenacres Rd. Oldham. Lancs ...........WW446

Two leaflets from Culan Electronics Ltd, By Ormíston, East Lothian, Scotland, describe a.c. power controllers up to 3 kW $\qquad$ .WW447

SE Laboratories (Engineering) Ltd, North Feltham Trading Estate, Feltham, Middlesex have available a leaflet which briefly describes the test equipment they produce $\qquad$ WW448

## New Products

## Flying Spot Scanner Tube

A new screen phosphor is used in the Mullard, five-inch, flying spot scanner tube type Q13-110GU. The tube has magnetic -focusing, a metal-backed screen, and a spark gap to prevent internal flashover between the anode and the grid. It operates with an anode voltage of 25 kV and has a resolution better than 1000 lines. The new phosphor, a cerium activated yttrium aluminate, has an emission peak at 550 nm and an extremely short decay time of less than $0.1 \mu \mathrm{~s}$. It is mixed with a blue phosphor (caesium activated ytrium silicate), which also has a short decay time. Because of the short decay time of the phosphors, the flying spot scanner tube can follow fast moving objects without blurr. Mullard Ltd., Mullard House, Torrington Place, London W.C.1.

WW 302 for further details

## Miniature Rotary Switch

Highland Electronics have announced a miniature rotary switch in the Highland/Grayhill range-series 53. The switches have the following features: up to


24 positions ( $15^{\circ}$ indexing angle); up to 12 decks; up to 12 poles per deck; diameter over tags 1.35 in ; gold plated contacts. Panel and spindle seals are available. Highland Electronics Ltd, 33-41 Dallington Street, London E.C.I.
WW 303 for further details

## Quick-heating Iron

The Ersa Sprint quick-heating soldering iron, made in West Germany, is available from Home Radio (Components). Warm up time is less than 15 seconds. When the press switch is released the iron starts to

cool, but remains sufficiently hot to continue to melt solder for about 1 minute. The technique for using it therefore seems to be to press the switch for 15 seconds, then release it just at the point of starting to make the soldered joint. The switch could be held down for the whole time of soldering, particularly if there was rapid heat conduction from the joint, but this would cause the bit to oxidise more rapidly. The iron proper weighs less than 5 ounces ( 7 ounces with lead and plug), and when laid down on the bench after use it is balanced so that the bit does not touch the bench. Although the iron is marked 220 V the suppliers state that it is suitable for all a.c. voltages from 220 V to 250 V and are prepared to guarantee it for use within this range. Spare parts are available and any part can be changed very quickly. Price $£ 3$ 19s 6d. Home Radio (Comsonents) Ltd, 234-240 London Road, Mitcham, Surrey, CR 4 3HD.
WW329 for further details

## Op. Amp Dual Output Supply

A dual output supply to power operational amplifiers is available from Lambda Electronics. The outputs are $\pm 12$ to 15 V d.c. at 400 mA for each line. The voltage difference between the lines is maintained to within $1 \%$ of absolute voltage or $0.1 \%$ change for all variations of line, load, and temperature. The unit, designated LXD-3-152, gives series connected dual outputs. Convection cooling is used and no external heat sinks or forced-air systems are required. Regulation is $0.1 \%$ of line or load; ripple and noise 1.5 mV r.m.s., 5 mV peak to peak. Remote sensing is provided. Current limiting is fixed and
current ratings at different operating temperatures are clearly specified. The unit measures $80 \times 95 \times 130 \mathrm{~mm}$. A 24 to 40 V version is also available. Lambda Electronics. Marshland Road, Farlington, Hants.
WW 318 for further details

## Lockjaw Vice

A vice, called the Lockjaw, has been introduced which is suitable for industrial or domestic use and incorporates a number of novel features. The vice has 104 mm ( $4 \frac{1}{16} \mathrm{in}$ ) jaws, is 200 mm ( 8 in ) long and $100 \mathrm{~mm}(4 \mathrm{in})$ high and weighs about 1.75 kg . The silicon metal jaws have indents and slots machined in them so that tubes and discs can be held without excessive pressure and therefore without damage. The jaws can be easily prised off and the rear jaw can be reversed (turned upside down). If this is done the rear jaw is free to pivot so that it automatically adjusts to the shape of any tapered objects that have to be clamped, again avoiding excessive damage. The vice as described above has a recommended retail price of 86s. For more delicate work rubber-faced jaws are available as an extra ( 14 s a pair). There are three ways of mounting the vice. In its standard form it can be bolted to a bench in the normal way. A suction base can be purchased (30s) which allows the vice to be firmly attached to any flat

non-porous surface without damaging the surface in any way. Finally a substantial G-clamp is available (30s) which can be bolted to the vice so that the vice can be mounted on any convenient bench, girder, etc. Vice and Workholding Co. Ltd, 149a Crayford Rd, Crayford, Kent.
WW 301 for further details.

## Spot-frequency Marine Receivers

Two multi-channel, single-sideband receivers are introduced by Eddystone Radio. Both have crystal-control and operate on switch-selected spot frequencies. One of these models, type EC964/1, provides a choice of 52 spot frequencies in the medium- and high-frequency bands, while the other, type EC964/3 offers a choice of 28 spot frequency channels in the m.f. maritime band. The two receivers meet the British Post Office specifications TSC 102 and TSC 105 respectively. The EC964/1 is primarily intended for use in ocean-going ships, while the EC964/3 is suitable for

ships operating in coastal waters where the higher frequencies are not normally used. Both receivers cover the international distress and calling channel ( 2182 kHz ), other frequencies being chosen by the customer before delivery. Channels are switch-selected to simplify operation. Reception facilities cover double-sideband and single-sideband voice transmission, upper-sideband being accepted in the latter mode. An integral monitor loudspeaker is fitted and outlets are provided for telephones and remote line circuits. Operation can be from any standard a.c. supply or from low-voltage d.c. using a G.P.O. approved d.c./a.c. converter type 978. GEC-Marconi Electronics, Eddystone Radio Ltd, Marconi House, Chelmsford, Essex.
WW330 for further details

## Modular Power Supplies

LTH Electronics have launched a series of compact, high specification stabilized power supply modules. Known as the LRA series, it is designed for installation into customers' equipment and is built as a 19in rack-mounting module. Both single and twin units are available with preset voltages in the range of $1-30 \mathrm{~V}$ and $30-50 \mathrm{~V}$ at $1,2,5$ and 10 A . The stability ratio is greater than $200,000: 1$ and typically $500,000: 1$. A fast acting, automatic-reset, over-current circuit affords complete protection against short circuit and overload. Remote sensing enables the correct voltage to be maintained at the load terminals and integral over-voltage units are available for the protection of

expensive external loads. The output resistance is less than $0.0005 \Omega$. Ripple and noise is less than $200 \mu \mathrm{~V}$. LTH Electronics Ltd, Eltelec Works, Chaul End Lane, Luton, Beds.
WW327 for further details

## Quartz-crystal Units

The McKnight Crystal Company supply a range of hermetically sealed, nitrogen filled, metal-cased AT-cut quartz-crystal units covering the frequency band 1400 kHz to 20 MHz . These units are available in several holder styles including miniature Def. types D, J and K. A wide range of frequency tolerances is available for oscillator or filter applications. Frequency calibration is to customers' requirements. McKnight Crystal Company, Unit 21, Shipyard Estate, Hythe, Southampton SO4 6DE.
WW333 for further details

## Function Generator

Model 142 HF VCG generator from Wavetek (available through Wessex Electronics) is a precision signal source with a frequency range of 0.0005 Hz to 10 MHz . In addition to sine, square and triangle waveforms model 142 offers a variable duty cycle on all output waveforms. This can be continuously adjusted from $5 \%$ through the usual $50 \%$ to $95 \%$. This means that pulse outputs can be generated with on-off ratios of $1: 19$, 19:1 or anywhere between. A sawtooth

waveform with a rise-fall ratio of 1:19. $19: 1$ is also possible. In addition to the 15 V pk -pk into $50 \Omega$, the 60 dB step attenuator allows clean signal levels as low as 15 mV (pk-pk). An external sweep signal (either d.c. programming or a.c. modulation) can be applied to sweep the output over a 1000:1 ratio. Square-wave rise and fall time is less than 20ns. Wessex Electronics Ltd, Stover Trading Estate, Yate, Bristol BSI 7 5QP.
WW332 for further details

## Time Scale Generator

The Comark time scale generator, type 1401, provides a 'rule-scale' timing waveform from $1 \mu \mathrm{~s}$ to 10 s with an accuracy of $0.005 \%$. There are three simultaneously available waveforms. The rule-scale waveform consists of equispaced

rectangular pulses of three distinct amplitudes, every fifth and tenth being accentuated without change of duration. An 8-position switch selects the scale by specifying the least significant interval. The unscaled outputs are 1:4 mark/space ratio pulses from seven separate outputs with periods from $1 \mu \mathrm{~s}$ to 1 s . The squarewave output has unity mark/space ratio and an interval of 10 times the periods indicated by the selector switch. The output stage has a rise time of 40 ns and a fall time of 30 ns . The internal 1 MHz reference can be replaced by an external clock signal for increased accuracy or to permit generation of long time periods. Two instruments, used in cascade, will generate periods up to $10^{8} \mathrm{sec}$. Comark Electronics Ltd, Brookside Avenue, Rustington, Littlehampton, Sussex.
WW 324 for further details

## 3.5-W Amplifier

A low-cost version of the General Electric (U.S.A.) PA246 5-W amplifier, the PA263, is available from Jermyn. Designed for supply voltages up to 30 V it will deliver 3.5 W r.m.s. continuously with about 9 mV input. It may be used with various supply voltages, loads and inputs by adjusting external components. Price for quantities $1-24$ is 33 s (plus 2 s 6 d post and packing for small orders). Jermyn Industries, Vestry Estate, Sevenoaks, Kent.
WW328 for further details

## Dual Pulse Stretcher

A noise-free pulse of almost any width can be generated by the type MC 675 pulse stretcher from Motorola. The width of the output pulse generated by this circuit is determined by the width of the input pulse and a time constant derived from an external capacitor and either an external or an internal resistor. Two modes of operation are made possible by the inclusion of a two-input NOR gate at the output. When the signal levels at both inputs of this gate are low and with the input pulse fed to the pulse-stretcher input terminal only, the unit operates as a
conventional pulse stretcher to generate a pulse the duration of which is related to the input pulse duration as described above. The unit can also operate as a monostable multivibrator. In this configuration, no output pulse is generated for an input noise pulse of a duration (in seconds) equal to 10 times the value of the external capacitor (in farads). Propagation delay is 110 ns and the power dissipation is 180 mW . Encapsulation is a plastic TO-116 package. The temperature range is -40 to $+75^{\circ} \mathrm{C}$. The price is 45 s each for quantities of 100 and above, Motorola Semiconductors Ltd, York House, Empire Way, Wembley, Middx.
WW331 for further details

## Printed Circuit Sockets

Oxley Developments Company have added a subminiature socket, type $30 \mathrm{~S} / 093 / \mathrm{PCB}$, to its range of miniature printed circuit sockets. Designed to accept the standard Oxley 30P/093 plug, the sockets mount on a standard 0.150 in $(3.8 \mathrm{~mm})$ module printed circuit board. Plugs are inserted in a plane parallel to the

printed circuit board to allow compact board stacking. Single or multiple units with up to ten outlets can be supplied: p.t.f.e., insulating bushes are available in eleven colours to BS 2746; socket contacts are gold-plated brass. Oxley Developments Co. Ltd, Priory Park. Ulverston, Lancs.
WW 313 for further details

## $\mathbf{5 0 - M H z}$ Digital Frequency Meter

Orbit Controls have announced the first of a new family of electronic instruments for 19in rack mounting with a panel height of only $1 \frac{3}{4}$ in. Digital frequency meter type $71 \mathrm{C} \quad 100$ is a direct reading 5 -decade instrument covering the spectrum 20 Hz to

50 MHz . Input sensitivity over the range is 10 mV , and the dynamic range is better than 60 dB . Three programmable gate times and four programmable display times are available. Selection of gate and display time is remotely programmed via a multipole socket on the rear panel. The instrument is designed so that it may be used to indicate the incoming frequency to a communications receiver by monitoring the local oscillator frequency. To provide direct reading, up to six frequency offsets are provided and the particular offset, equal to the receiver intermediate frequency, may be selected to add to or subtract from the local oscillator frequency as appropriate. Selection of frequency offset is, again, remotely programmed via a multipole socket on the rear panel. The front panel of the instrument is clear of controls other than a test button which enables the quartz crystal derived timing signal to be switched to the input circuit. Input, outputs. switch, etc., are located on the rear panel. The display module may, if required, be removed from the instrument and connected by an external cable to a further socket on the rear panel to provide a display remote from the instrument. An alternative version, type 71 C 101 , is also available, having gate and display times selected by means of front panel push-buttons. In this version the frequency offset, if required, is prewired internally. In other respects the two instruments are identical. Orbit Controls Ltd, Alstone Lane Industrial Estate, Cheltenham, Glos. GL51 8JQ.

## WW 309 for further details

## Low-cost Dry Reed Relays

A range of dry reed relays has been introduced by ITT Components Group Europe. The HRE 399, HRE 599, HRE 899 and HRE 831 are low-cost general-purpose industrial relays incorporating up to four "normally open" (make) switches. They are designed for printed-circuit mounting on boards up to 2.5 mm thick, with the mounting lugs and electrical terminals being on a grid spacing of 2.54 mm . The depth of the relays is 10.5 mm , and magnetic and mechanical protection is provided by a metal shield. The HRE 399 relay has a maximum switching current of 0.6 A a.c. $/ \mathrm{d} . \mathrm{c} .$, maximum switching voltage of 220 V a.c. /d.c. and a maximum switching power of 12 VA . Maximum switching current for the HRE 599 is 1A a.c./d.c.; the maximum switching voltage is 250 V a.c.

or 90 V d.c. and the maximum switching power is 24 VA . For the HRE 899 relay the maximum switching current is also 1 A a.c./d.c., with the maximum switching voltage being 250 V a.c. or 150 V d.c. and the maximum switching power 60 VA . The HRE 831 has the same performance as the HRE 899 relay. ITT Components Group Europe, Power Components Division, West Road, Harlow, Essex. WW 308 for further details

## Signal Amplifier

The Bournlea Dynamic d.c.-a.c. amplifier has a bandwidth from d.c. to 500 kHz , 25 V pk-pk output swing and employs f.e.t. input stages to provide a drift of less than $50 \mu \mathrm{~V} /{ }^{\circ} \mathrm{C}$ and a noise level of $25 \mu \mathrm{~V}$ r.m.s. at 60 dB gain. Alternative overall gain settings of 0,20 or 40 dB are selectable by switch, the gain accuracy being 0.5 dB . The $1 \mathrm{M} \Omega$ input resistance is accurate within $\pm 2 \%$ and makes it possible to use the amplifier as an accurate high gain current to voltage converter down into the nA and pA region. Either a.c. or d.c. input coupling can be selected, the low frequency cut-off being at 1 Hz in the a.c. mode. The output d.c. potential is adjustable by a single front panel control the setting of which is unaffected by the input source resistance. The output resistance is less than $20 \Omega$. Operation is from self-contained batteries. The amplifier is available from The Cardon Instrument Co., Earls Colne, Colchester, Essex.
WW 307 for further details

## Modular Pulse Generator

The Bradley Modular Pulse Generator 176 is a 50 MHz instrument for generating various complex pulse patterns. The use of modules in a basic main frame provides flexibility-the modules can be arranged in any order and additional units added as required. The main frame which

includes the stabilized power supply, can accommodate up to 11 modules. These are interconnected by coaxial cables. Six modules are currently available. the basic units being a period module capable of producing any p.r.f. from 1 Hz to 50 MHz , and a delay/width module providing pulse widths or delays from 10 ns to 1 s . Other modules include a high-impedance variable-level input unit, and an output module providing up to 6 V and having a risetime of 2 ns . Fan-in and fan-out units provide expansion, pulse-width subtraction. and inversion. Separate sockets are used for each interconnection, and all outputs are short circuit proof. G. \& E. Bradley Ltd, Electral House. Neasden Lane, London, N.W. 10.
WW 326 for further details

## Square Trimmer Resistor

Reliance Controls have introduced a new $\frac{1}{2}$-in square wirewound fully sealed trimmer. The trimmer is available in three versions, designated CW65. CW66 and CW67, dependent upon the pin configuration required. Suitable for printed circuit board mounting, the various styles allow the designer to make the maximum use of available space. Resistance range of the CW65 /66/67 trimmers covers $10 \Omega$ to $25 \mathrm{k} \Omega$. Mechanical adjustment is 25 turns and temperature range -55 to $+155^{\circ} \mathrm{C}$. Wattage rating (whole element uniformly

loaded) is 1 W at $20^{\circ} \mathrm{C}$, derating to zero to $155^{\circ} \mathrm{C}$. Insulation resistance is $1000 \mathrm{M} \Omega$ at 500 V d.c. The wiper is of gold plated beryllium copper, and the terminals are gold plated. Reliance Controls Ltd. Drakes Way, Swindon, Wilts.
WW 316 for further details

## Centre-tap <br> Silicon Diode Assemblies

The Semiconductor Division of Westinghouse Brake and Signal Co. have introduced a series of silicon double-diode rectifiers rated at 20 A with voltage ratings of $100-600 \mathrm{~V}$. This series of centre-tap assemblies is designated


SxRC10 and SxRN10. Higher than usual overload to mean-current rating ratio is claimed. Housing is a standard TO-3 glass/metal package which permits mounting on normal transistor heat sinks. Westinghouse Brake and Signal Co. Ltd. 82 York Way, King's Cross, London N. I. WW 306 for further details

## Thyristors for High-frequency Inverters

Two new families of thyristors available from Mullard have high $d i / d t$ and $d v / d t$ ratings of $100 \mathrm{~A} / \mu \mathrm{s}$ and $200 \mathrm{~V} / \mu \mathrm{s}$ respectively with crest working voltages of 800,1000 , and $1,200 \mathrm{~V}$. Types BTW23 and BTW24, are p-gate, reverse blocking. avalanche devices intended for use in high-frequency inverters and motorcontrol circuits. The BTW23 thyristors have a maximum forward current rating of 70 A and an avalanche rating of 40 kW when a square pulse of $10 \mu$ s duration is applied and the junction temperature is $25^{\circ} \mathrm{C}$. The thyristors have an encapsulation
similar to the TO-49 with an M12 thread. on the stud. The BTW24 thyristors have a forward current rating of 30 A and an avalanche rating of 20 kW ( $10 \mu \mathrm{~s}$ square pulse when junction temperature is $25^{\circ} \mathrm{C}$ ). These thyristors are contained within TO-103 encapsulations. Mullard Ltd, Mullard House, Torrington Place, London W.C.1.

WW 322 for further details

## 100-W Power Transistor

Microwave Associates have announced the first $100-\mathrm{W}$ power transistor at 1 GHz , designed specifically for pulse applications. The device will provide 10 dB gain as an amplifier, and 60 watts output as an oscillator, at 1 GHz . Microwave Associates Ltd, Cradock Road, Luton, Beds.
WW 310 for further details

## Corona Stabilizers

The M-O Valve Company has extended its range of metal/ceramic corona stabilizers with the introduction of the SC8 and SC9 series. The SC8 (the larger in the photograph) provides stabilized voltages in the range 25 to 50 kV in six 5 kV stages and the SC9 in the range 350 to 2000 V in 11 stages of from 50 to 200 V . Specific voltage types can also be made to

customers' special requirements. After one minute the voltage remains constant to within $0.25 \%$ of the initial value for at least two hours. and long-term stability is better than $1 \%$ per 1000 hours. The temperature coefficient of the SC 8 is $0.005 \% /{ }^{\circ} \mathrm{C}$ while for the SC 9 it is measured at $0.3 \mathrm{~V} /{ }^{\circ} \mathrm{C}$ over the temperature range -40 to $+90^{\circ} \mathrm{C}$. The M-O Valve Co. Ltd, Brook Green Works, London W.6.
WW 323 for further details

## Microwave Duplexer

Type MCH5890 microwave duplexer from Motorola consists of two

step-recovery diodes. one connected in series between the transmitter terminals and the receiver terminals, and the other one shunting both pairs of terminals. The device can accept a 40 W input power. During transmission the insertion loss between aerial and transmitter terminals is only 0.1 dB while the isolation between the aerial and receiver terminals is 25 dB . Motorola Semiconductors Ltd, York House, Empire Way, Wembley, Middx.
WW 319 for further details

## M.O.S. Arrays for Electronic Organs

Two m.o.s. arrays specifically designed for electronic organs are available from WEL. Array type MA70 is a ${ }^{12} \sqrt{2}$ divider giving true semi-tones. Array type MA60 is a six-stage binary divider giving six outputs each one octave apart. (An electronic organ can be made with four MA70 circuits and twelve MA60s.) For organ designers requiring a free-phase system 30 MA 70 s could be used. Prices are about $£ 310 \mathrm{~s}$. for the MA70 and 25 s for the MA60 (for quantities in excess of 1,000 pieces). WEL Components Ltd, 5 Loverock Road, Reading, Berks.
WW 320 for further details

## Lightweight X-band <br> Travelling-wave Tube

The M-O Valve Company has introduced a low-cost lightweight X -band travelling wave amplifier, type TWX34. giving a minimum gain of 35 dB and a saturated power output of 1 W over the frequency range 7.5 to 11 GHz . A typical application is in the ground station of a transportable satellite communications system where continuous operation in ambient temperatures of up to $60^{\circ} \mathrm{C}$ and ability to withstand shock, vibration and high humidity conditions are required. A low wattage oxide coated cathode has been incorporated and total power supply consumption under full r.f. drive conditions is less than 25 W . Power supply connections are by flying leads, but other

types of connection can be provided on request. The M-O Valve Co. Ltd. Brook Green Works, London W. 6.
WW 321 for further details

## Switching Diode

A silicon planar. epitaxial, whiskerless diode, type BAV44, is announced by Mullard. It can rapidly switch currents up to 1 A , and is primarily intended for use in servo amplifiers. digital voltmeters and oscilloscopes. Maximum continuous

reverse voltage is 65 V and the maximum voltage drop with a forward current of 1 A is 1.25 V . Switching time $\left(t_{r r}\right)$ from $I_{F}=$ 1.0 A to $I_{R}=1.0 \mathrm{~A}$ and measured at $I_{r r}$ $=100 \mathrm{~mA}$ is 22 ns . Diode capacitance is 7.5 pF . Mullard Ltd, Mullard House, Torrington Place, London W.C. 1.
WW 325 for further details

## Integrated Circuit Socket

Employing a new concept in socket design for integrated circuits and semiconductor devices, the A23/2033 now available from Jermyn, is a 25 -contact single strip socket capable of accepting either flat or round

leads. The body of glass-filled nylon is fitted with gold flash phosphor bronze contacts, giving a life of up to 10,000 insertions with an electrical resistance of $15 \mathrm{~m} \Omega$. Jermyn Industries, Vestry Estate, Sevenoaks, Kent.
WW 305 for further details

## Oscillator Klystron

A forced-air cooled, fixed frequency, two cavity oscillator klystron (K3071), for operation in airborne Doppler and beacon radar equipment, has been introduced by English Electric Valve Co. The tube incorporates a heater design claimed to give a lower level of heater f.m. than

hitherto attainable. In addition, the sturdy construction results'in a tube having low noise and low microphony. A further improvement is its longer life expectancy compared with earlier types. Operating frequency of the K 3071 is $8800 \pm 5 \mathrm{MHz}$ and a typical output power is 1.5 W , but variants can be supplied for operation at any frequency in the 8 to 9.5 GHz range. Silicone rubber moulded connections are used for unpressurized high-altitude operation. English Electric Valve Co. Ltd. Chelmsford, Essex.
WW 315 for further details

## Solid-state Plus/Minus Sign

To indicate plus or minus information, a light-emitting diode display module has been added to Hewlett-Packard's numeric indicators. The model 5082-7018 plus/minus sign comes in the same package as the 5082-7000 series of numeric indicators. It operates at less than


5 V . A plus or a minus is displayed by applying a drive voltage to one (minus sign) or two (plus sign) input leads. A third lead is the earth connection. Brightness can be varied by changing the d.c. drive between 1.6 and 4 V . Hewlett-Packard Ltd, 224 Bath Road, Slough, Bucks.
WW 317 for further details

## Schmitt Trigger I.C.

SN7413N Schmitt trigger combines two 4-input positive nand gates. Each gate has different input levels for positive and negative going signals. Hysteresis (the difference between two threshold levels) is typically 800 mV . Noisy pulses can be accommodated without false trigger regardless of change of temperature. The units also fire reliably with rise and fall times slower than 1 V per second. The unit is housed in a 14-pin dual-in-line plastic package and costs 10 s 1d each in quantities of 100 . WEL Components Ltd, 5 Loverock Road, Reading, Berks.
WW 311 for further details

# "Have we eaten of the insane root that takes the reason prisoner?" 

Now that the dust of the General Election has settled, with the computers, both electro-mechanical and human, duly confounded,* we are now looking forward with differing degrees of trepidation to the delights the future holds under our new masters.

The political parties are unanimous in plumping for increased production for export as the prime means of salvation. This being so, I thought that for a few minutes we might do worse than to take a look at our own electronics industry to see whether anything could be done to improve existing performance.

The position of industry in general can be likened to that of a farmer who possesses twenty cows. Under Communisn, the State takes the cows and sells some of the milk back to the farmer. Labour buys the milk from the farmer and pours it down the drain. The Conservative policy is to get the farmer to sell five cows and buy a bull. The Liberal outlook is much the same except that they would employ A.I. All, however, subscribe (by implication at least) to the premise that the bigger the organization the more efficient it is; so the trend has been towards the scooping of a multitude of little electronics concerns into a few gigantic ones.

We all know the arguments for mergers-streamlining, rationalization, the avoidance of duplication of effort, are all stock phrases-but, according to a recently published study, $\dagger$ most takeovers and mergers are made for the security and convenience of the management of the bidding company. Usually (it says) the major motives are to gain bigger shares of their markets, reduce competition or protect themselves from other predatory firms.

Be that as it may, the concept that the greater the size, the greater the efficiency, is rubbish, and those who argue for it take no account of human nature. As an instance, those of you who run your own small businesses won't need to be told that economies in small matters make the difference between extracting a living and going broke.

[^3]Not so in the big organization. To the clerk who is writing a letter about a $£ 250,000$ order, a second sheet of paper is too trifling a matter to be considered and it is far too easy to reach for a telephone to save the fag of writing.

In such circumstances the management's typical reaction is either nil, which is bad, or to create a Gestapo department to deal with it, which is often worse. Control departments of this character are frequently parasitic growths, sucking out an existence from the main stem of profits, for they can, all too easily, cost more to maintain than the savings they effect.
A typical example of the control system now in vogue is P.E.R.T. (the initials stand for Programme Evaluation and Review Technique). In essence this is a semidiagrammatic method of ensuring that all the bits and pieces for a large contract come together at the right times and places so that the job flows smoothly to completion on schedule. It also sets out to keep tabs on costs and to aid the solution of various management problems. It is the sort of thing that no trendy company would dream of doing without, on the grounds that present-day systems orders are on so large a scale that it would be impossible to control them efficiently in any other way. But some while ago I was at a gathering which included several veteran engineers and I was amazed to hear from one of them of the size and complexity of some of the radio communication systems which were undertaken between the wars, and even back in the 1914-18 period. Nobody had ever heard of P.E.R.T. in those days, but the jobs got done in far quicker time than they would take today. At that time it was part of engineering training to be able to visualize the demands for materials well before they arose, and to order accordingly. The man who couldn't do that didn't become a senior or chief engineer or if he did, he didn't last long. He was sacked.

Now P.E.R.T. in principle is applied commonsense and, used rationally, is well enough. It is at its interface with human nature that it can fall down badly. Elevate it to the status of a department and it can so easily become a coterie of high priests whose main-although perhaps uncon-scious-aim is to preserve the mystique and to enlarge the sphere of influence of
the cult.
The computer is another control system which is wide open to misuse. Computers tend to be run by an alien race of high priests who, protected from close investigation by reason of the jargon of their calling, can easily let enthusiasm outweigh sober judgement and advocate the use of highly expensive machines for jobs that a desk calculator could do in less time and at a fraction of the cost.

A big combine tends to be riddled with control departments; all were instituted with the best of intentions; some, possibly, save the company money. But it would at any rate do no harm for such a firm to take a cool, hard look at all such areas to see whether they are costing more to maintain than the amounts they save. The grave danger, too, with efficiency-control systems is that they can easily become a cloak for managerial ineptitude and face-saving. When things go wrong their presence can make the difference between the personal admission of "I was to blame" and the shrugging-off comment "Unfortunately there was an undetected error in the computer programming". Such an outlook leads by logical progression to the present prevalent practice of calling in an external firm of management consultants to advise on company reorganization. By definition a manager's function is to manage, and do so to such effect that he makes a profit for his company. If he cannot do this, then he should go.

Are we, in fact, making too much of a fetish of large-scale electronics groupings and business efficiency systems? These approaches of course are an aping of American techniques, but what is sauce for the American goose is not necessarily sauce for the British gander; it should not be forgotten that, in spite of its size and vaunted efficiency, the American electronics industry would collapse like a house of cards if disarmament became a reality and government-sponsored space programmes were stopped.

Now I come to think of it, the humble tea-break is, in its way, symptomatic of the whole business of pseudo-efficiency. Time was when the tea-lady and her trolley did the rounds twice daily, dispensing cheer to all. But, "Inefficient!" said the experts, and proceeded to prove on paper how much cheaper machines would be. "Splendid!" said management and so it came to pass that machines were installed and the tea-lady was out.
After the inevitable teething troubles, things go famously for a while and the revenue rockets. Management rubs its hands, overlooking the fact that a timesthree increase in takings signifies that a considerable proportion of the proletariat are now taking several tea-breaks per diem instead of the statutory two.

This bit of automation was originally an American idea which has been widely copied over here. But one world-famous firm has, to my certain knowledge, seen the light and has gone back to the oncederided trolley. I hardly like to mention this, but it's located in the U.S.A.

## Outline details of some up-to-date units

It is fair to suggest that the poor relation of most hi-fi enthusiasts' systems is the radio tuner, if indeed a tuner is included at all.

While at any time the upper crust of the hi-fi fraternity are willing to enter into protracted and sometimes pretentious discussion of purely mechanical parameters such as wow and flutter, mass, compliance, trackability and so on, radio reception is hardly regarded by some as worthy of consideration. Yet this latter via the radio tuner is a truly electronic signal source that could be more actively utilized. Most of the country is now covered by v.h.f. transmitters so that it is possible for the majority of listeners to receive a reliable signal*. If the transmission is a "live" one originating in a studio local to the transmitter, the output from a hi-fi system can be of superbly high quality, especially on stereo.

Hi-fi probably came into its own as a "following", with the introduction of the LP disc and thus made possible music quality in the home far superior to that supplied by long- and medium-wave a.m. radio. But medium-wave radio has nothing to do with hi-fi and it is only at v.h.f. with f.m. transmissions that radio, mainly because of better noise performance at those frequencies, can compete with the record. It is true that some manufacturers supply an a.m./f.m. tuner with medium-, long- and sometimes short-wave reception, in addition to the v.h.f. band. However, no one pretends that quality programmes are possible on the a.m. bands and these are usually included merely to give maximum coverage of the available transmissions, since the v.h.f. band provides only B.B.C. programmes Radio 2, 3 and 4, and some local radio. Also v.h.f. has limited area coverage and foreign programmes generally can only be received on a.m. bands.

## Importance of tuning

The distortion content of an f.m. transmission is potentially extremely small. One particu lar requirement to avoid distortion on f.m. is accuracy of tuning. Unlike the simple a.m. demodulator, if the i.f. signal is not centred on the linear portion of the f.m. discriminator

[^4]characteristic the demodulated audio signal will be non-linear. Again unlike a.m. reception it is not easy with an f.m. tuner for the listener to find the centre frequency by ear and most tuners feature visual and automatic electronic facilities to assist in tuning and to prevent oscillator drift with time.

## Sensitivity and noise

It is in the matter of audio dynamic range and signal-to-noise ratio that disc recordings could be said to be superior to that of broadcast signals. Because of the need to maintain the broadcast signal at a reasonably high average it is necessary for the B.B.C. to limit the audio dynamic range (the range from the softest to the loudest passage) to a particular ratio; $30-35 \mathrm{~dB}$ having been quoted. Recordings have not the same limitations of dynamic range. On the question of noise, one big advantage of the f.m. system over a.m. is that extraneous signals which display an a.m. characteristic can be removed from the input signal by a limiter circuit. These include static and man-made interference such as that caused by ignition systems and electrical apparatus. By limiting the maximum amplitude of all signals, the discriminator is presented with a signal of constant amplitude, with variations in frequency only.

Random noise (white noise) contains a.m. and f.m. components and the f.m. when detected is heard as a background noise or hiss. Because of the nature of f.m. detection and the use of a.g.c. circuits the audio output from the detector is reasonably constant and the difference between strong and weak stations manifests itself by the amount of background noise present. To obtain good clean reception (and the worst is always cleaner than a.m.) it is desirable for the tuner to enjoy good sensitivity and low noise when the amplifying stages are working at high gain. This "usable" sensitivity is invariably quoted by tuner manufacturers as so many $\mu \mathrm{V}$ for so many dBs quieting, for example: $2 \mu \mathrm{~V}$ for 30 dB quieting being typical.

Noise increases as the audio frequency range is extended, and this is counteracted by emphasizing the high-frequency end of the audio range before transmission and
de-emphasizing by the same amount in the receiver. By this means the frequency response effectively remains level but the accompanying noise is attenuated. The de-emphasis figure is quoted as $50 \mu \mathrm{sec}$ which represents the time-constant of the de-emphasis circuit.

As has been stated then the greatest advantage of f.m. over a.m. is the virtual elimination of interference and this combined with transmissions at v.h.f. has allowed a greater audio bandwidth. Some programmes, however, which are routed over many miles of land-line networks before reaching the transmitter, suffer from attenuation of the high frequencies. The U.K. system bandwidth is 15 kHz with a deviation frequency of $\pm 75 \mathrm{kHz}$. The ratio of deviation frequency to the highest audio frequency (deviation ratio) has a direct influence on noise performance $\dagger$. The i.f. bandwidth of an f.m. tuner is typically 200 kHz at the 6 dB points. The response should be symmetrical, and the linear portion of the discriminator characteristic should cover at least 100 kHz to prevent distortion. (Grundig claim for their RT100 tuner that the distortion factor is below $1 \%$ when it is detuned by 50 kHz .) Although present-day tuners are very sensitive and can be operated from relatively crude aerial installations, distortion can arise as a result of multipath reception and for this reason alone it is wise to consider the erection of an efficient outdoor aerial preferably with some directional properties. All v.h.f./f.m. transmissions are horizontally polarized which means that even the simple dipole offers some rejection of reflected signals on a horizontal plane but "aircraft flutter" can be troublesome in some areas. A particularly unpleasant form of distortion can occur from reflected signals which makes piano music sound as if the speaker windings were dragging the magnet pole piece.

## Basic requirements

Having settled on a suitable aerial, all that is necessary for enjoyable reception on an existing hi-fi amplifier and speakers is a quite simple, well designed tuner. It

[^5]should have good sensitivity so that the limiter is always saturated, adequate bandwidth with good response, a stable oscillator and a discriminator with a high order of linearity. To save further on cost the tuner could be powered from the main amplifier if the amplifier power supply ratings allow but for convenience it is better to buy a tuner unit with its own mains power unit. Such a tuner can be obtained for a modest sum. If stereo reception is required the tuner must incorporate a stereo decoder. Most modern tuners are suitable for stereo
reception but if cost is a prime factor a "stereo ready" tuner could be purchased and used on mono. It could be converted to stereo at a later date by means of a plug-in decoder module available from the manufacturer.

Refinements on the more expensive tuners are extras which improve reception in weak-signal or difficult areas and electronic aids to relieve the user of a certain amount of guesswork. Among these are visual tuning indicators which may take the form of an ordinary meter movement, an electronic tuning eye or

## Stereo test tone transmissions

To facilitate channel identification and adjustment of channel cross-talk a 250 Hz tone is transmitted every day except Wednesday and Saturday in the left channel only from about four minutes after the end of Radio 3 until 23.55. This test may be interrupted from time to time. On Wednesday and Saturday the following test sequence is transmitted by the B.B.C.

| Test No. | Time (Approx.) | Left channel (A) | Right channel (B) | Purpose |
| :---: | :---: | :---: | :---: | :---: |
| 1 | 23.42 | 250 Hz at zero level | 440 Hz at zero level | Identification of left and right channels and setting of reference level |
| 2 | 23.44 | 900 Hz at +7 dB | 900 Hz at +7 dB , antiphase to left channel | Adjustment of phase of regenerated subcarrier and check of distortion with signal wholly in the ( $A-B$ ). i.e. S. channel |
| 3 | 23.48 | 900 Hz at +7 dB | 900 Hz at +7 dB , in phase with left channel | Check of distortion with signal wholly in the ( $A+B$ ). i.e. M, channel |
| 4 | 23.49 | 900 Hz at +7 dB | No modulation | Check of A to B cross-talk |
| 5 | 23.50 | No modulation | 900 Hz at +7 dB | Check of B to A cross-talk |
| 6 | 23.51 .20 | Tone sequence at -4 dB : $\begin{array}{r} 60 \mathrm{~Hz} \\ 900 \mathrm{~Hz} \\ 5 \mathrm{kHz} \\ 10 \mathrm{kHz} \end{array}$ <br> This sequence is repeated | No modulation | Check of A-channel frequency response and $A$ to $B$ cross-talk at high and low frequencies |
| 7 | 23.52 .20 | No modulation | Tone sequences as for left channel on Test 6 | Check of B -channel frequency response and $B$ to $A$ cross-talk at high and low frequencies |
| 8 | 23.53.20 | No modulation | No modulation | Check of noise level in the presence of pilot tone |
|  | 23.55 | Reversion to monophonic transmission |  |  |

The schedule is subject to variation or cancellation to accord with programme requirements and essential transmission tests.

The zero level reference corresponds to $40 \%$ of the maximum level of modulation applied to either stereophonic channel before pre-emphasis. All tests are transmitted with pre-emphasis. Periods of tone lasting several minutes are interrupted momentarily at one-minute intervals.
With receivers having separate controls of subcarrier phase and cross-talk, the correct order of alignment is to adjust first the subcarrier phase to produce maximum output from either the A or the B channel during test-2 and then to adjust the cross-talk (or 'separation') control on tests-4 and -5 for minimum cross-talk between channels.
With receivers in which the only control of cross-talk is by adjustment of subcarrier phase, this adjustment should be made on tests-4 and -5.
Adjustment of the 'balance' control to produce equal loudness from A and B loudspeakers, is best carried out when listening to the announcements during a stereophonic transmission, which are always made from a centre-stage position. If this adjustment is attempted during the tone transmissions, the results may be confused because of the occurrence of standing-wave patterns in the listening room.

The outputs of most receivers include significant levels of the 19 kHz pilot tone and its harmonics. These components do not interfere with normal listening but do affect most signal-level meters. It is essential, therefore, to provide filters with adequate loss at these frequencies if instruments are to be used for the above tests.
even a system of coloured lights to indicate which side of the centre frequency the tuner is off-tune and when it is on-tune. Probably the largest single influence on good stereo quality is the decoder itself. Manufacturers favour different methods of extracting the left and right-hand channels from the composite signal but a point to watch out for here is the degree of channel separation. This should be typically 30 dB at 1 kHz .

In the early days of stereo transmissions some tuners gave a visual indication of when a stereo signal was present and it was then necessary to switch the tuner manually to stereo. Nowadays it is more usual for the stereo signal to switch-in the decoder automatically, at the same time lighting a pilot lamp to indicate that stereo is being received. Many tuners with automatic switching still retain a manual mono override switch because in fringe reception areas or situations where the stereo signal is very weak it may be preferable to hear the programme in mono with less background noise, which is the case when the decoder is muted. It should be mentioned that stereo transmissions in any case contain more noise than mono transmissions when received on a mono tuner because the audio information occupies slightly less of the carrier modulation depth.

To assist listeners in setting up their equipment correctly, the B.B.C. transmits special test signals at scheduled times. Details of these are set out in cols. 1 and 2 opposite.

If it appears that we are dwelling too long on the possibility that programmes are likely to be degraded by noise let us put things in perspective by saying that in the poorest conditions the noise on f.m. is less than is the norm on a.m., especially after dusk. With a "usable" signal, noise on f.m. is virtually inaudible.

## Use of new devices

Noise performance has again been improved as of late by the use of field effect transistors. These devices also make it easier to apply automatic gain control than do bipolar transistors and for these and other reasons many makers use an f.e.t. as an r.f. amplifier. Ceramic filters in place of conventional i.f. transformers are coming in and so too are i.cs. The use of i.cs no doubt eases production problems and ceramic filters can be designed with wideband characteristics and sharp cut-off to provide the necessary selectivity without the use of a large number of tuned circuits in the i.f. stages.

More and more manufacturers are now employing capacitance-diode tuning. This allows the ganged tuning capacitor to be dispensed with and tuning to be carried out by a single potentiometer. Sometimes four or more potentiometers are included, each with a separate tuning scale and press-button thus allowing the user to preset his tuner to four or more stations.

Oscillator frequency drift is corrected in most f.m. tuners by an automatic frequency control circuit (a.f.c.) which has
a pull-in range of some $150-200 \mathrm{kHz}$. Provision is commonly included to switch-out the a.f.c. so that the correct tuning point can first be found without the masking effect of the automatic tuning, which is then switched-in to take care of drift. Some listeners may wish to receive an f.m. station in an adjacent transmission area or those living in south-east coasta regions may sometimes receive Continental f.m. stations. These transmissions are necessarily much weaker than the local station and it is useful to be able to switch-out the a.f.c. in this situation to prevent the tuner being "captured" by the strong local signal.

## Available units

We circulated all known makers and suppliers of f.m. tuner units in the U.K. for details of their products and from each of those who replied we have selected one model for a short review in the following pages. We stipulated that the tuner must have a v.h.f./f.m. band but it could also cover a.m. bands. Unless stated otherwise the tuners mentioned are for a.c. mains operation. Tuner /amplifiers are excluded. Some specifications are suffixed (I.H.F.) where this has been given on the particular manufacturer's returns. It may well be however, that some unmarked specifications for tuners from other manufacturers are also to I.H.F. requirements but have not been so defined. I.H.F. are the initial letters of an American body, the Institute of High Fidelity, which lays down methods of measurement for audio equipment. In some cases it can provide for enhanced published performance figures.

Prices quoted are the suggested retail prices in force at the time of going to press, and include purchase tax.

Arena F211 (f.m. stereo)


Sensitivity: $3 \mu \mathrm{~V}$ for 20 dB quieting at 40 kHz deviation.
I.F. bandwidth: 250 kHz .

Discriminator bandwidth: 600 kHz .
A.M. suppression: better than 50 dB , limiting from $4 \mu \mathrm{~V}$.

Frequency response: $20-15000 \mathrm{~Hz}$.
Channel separation: better than 30 dB ( $250-6300 \mathrm{~Hz}$ ) Carrier suppression: better than 50 dB Price: 35 gn .
Automatic stereo switching with indicator and mono override switch; switched a.f.c.; capacitance-diode tuning with five press-buttons and scales. U.K agents: Highgate Acoustics, 184-188 Great Portland Street, London W.1

## Armstrong 524

(f.m., decoder optional)


Sensitivity: $1.5 \mu \mathrm{~V}$ (mono), $5 \mu \mathrm{~V}$ (stereo) for $30 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio at 75 kHz deviation. Limiting: Full limiting at $5 \mu \mathrm{~V}$. I.F. bandwidth: 220 kHz at 6 dB .
I.F. rejection: 90 dB .

Aerial inputs: $70-80 \Omega$ and $300 \Omega$.
Output voltage: 300 mV (average).
Output impedance: $1 \mathrm{k} \Omega$.
Price: $£ 404 \mathrm{~s} 6 \mathrm{~d}$.
When decoder is fitted, channel separation is 30 dB at 1 kHz , suppression at 38 kHz is 40 dB ; automatic switching and stereo indicator; tuning meter and interstation noise suppression. Armstrong Audio Ltd, Warlters Road, London N.7.

## Bush (a.m./f.m. stereo)



Sensitivity: $3 \mu \mathrm{~V}$ for $26 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio (mono).
Aerial input: not quoted.
Output voltage: 2 V (max).
Output impedance: $1 \mathrm{M} \Omega$.
Power supply: external from Bush stereo amplifier via 5 -pin DIN type socket.
Price: $£ 36$ 15s.
Tuner intended primarily for use with Bush stereo amplifier. Features a.f.c. on f.m. with switch; stereo indicator and tuning meter. Above details refer to f.m. section. Coverage on a.m. is long- and medium-wave bands with internal ferrite
rod aerial. Rank Bush Murphy Ltd, Power Road, Chiswick, London W.4.

Beomaster 5000 (f.m. stereo)


Sensitivity: $0.8 \mu \mathrm{~V}$ for $20 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio, 75 kHz deviation.
I.F. bandwidth: 200 kHz at 3 dB .

Detector bandwidth: 1 MHz .
Crosstalk: 40 dB at 1 kHz .
Aerial input: 75-300 .
Output voltage: adjustable between 55 mV and 1 V .
Pilot and carrier suppression: 50 dB .
Price: $£ 105$ (teak), $£ 106$ (rosewood). Ceramic filters and f.e.t. r.f. amp. and mixer incorporated; a.f.c.; automatic stereo switching with level adjustable between 1 and $100{ }_{\mu} \mathrm{V}$; interstation muting.
Bang \& Olufsen U.K. Ltd, Eastbrook Road, Gloucester GL4 7DE.

Dual CT16 (a.m./f.m. stereo)


Sensitivity: $1.5 \mu \mathrm{~V}$ for 26 dB quieting at 22.5 kHz deviation (mono).

Image rejection: 50 dB .
I.F. bandwidth: 200 kHz .

Channel separation: better than 45 dB . Pilot tone suppression: better than 50 dB .
Aerial input: $240 \Omega$.
Output voltage: 0.8 V for $30 \%$
modulation.
Output impedance: $47 \mathrm{k} \Omega$.
Price: $£ 106$.
Automatic stereo switching and stereo indicator; audio response $40-15000 \mathrm{~Hz}$ $\pm 1.5 \mathrm{~dB}$. Above details refer to f.m. section. On a.m. frequency coverage is $150-350 \mathrm{kHz}$ (l.w.), $500-1650 \mathrm{kHz}$ (m.w.), $6.7-15.4 \mathrm{MHz}$ and $5.6-6.6 \mathrm{MHz}$. Dual Electronic Industries, St. Georgen House, Mill Road, Stockenchurch, Bucks.

## Eagle AFT60 (a.m.ff.m. stereo)

Sensitivity: $2 \mu \mathrm{~V}$ for 20 dB quieting (stereo).
Channel separation: 28 dB at 1 kHz . Image rejection: 55 dB .
Aerial input: $75 \Omega$ unbalanced. Output voltage: variable $0-280 \mathrm{mV}$.
Price: £53 18s 10d.
Above details refer to f.m. section. Cover-

age on a.m. $600-1600 \mathrm{kHz}$ (m.w.) with sensitivity of $500 \mu \mathrm{~V}$. Teak cabinet; f.e.t. front end. U.K. agents: B. Adler \& Sons (Radio) Ltd, Coptic Street, London W.C.I.

## Elizabethan System 4 <br> (f.m. mono)



Sensitivity: $14 \mu \mathrm{~V}$ for 3 dB from limiting. Output voltage: 100 mV .
Price: £28
A.f.c. $\pm 250 \mathrm{kHz}$ range. Part of the Elizabethan Coniston Suite. Lee Products (Great Britain) Ltd, 10-18 Clifton Street, London E.C.2.

## Grundig RT100

(a.m./f.m. stereo)


Sensitivity: $1.5 \mu \mathrm{~V}$ for 26 dB quieting at 15 kHz deviation.
Image rejection: $58-66 \mathrm{~dB}$.
I.F. bandwidth: $160-200 \mathrm{kHz}$.

Discriminator bandwidth: 650 kHz .
A.M. suppression: better than 58 dB at 1 kHz .
Pilot tone suppression: 40 dB at 19 kHz , 60 dB at 38 kHz .
Channel separation: 35 dB minimum at 1 kHz .
Aerial input: $240 \Omega$.
Output voltage: 0.65 V for 40 kHz deviation.
Output impedance: $2 \mathrm{k} \Omega$ (lowest permissible load impedance $22 \mathrm{k} \Omega$ ).
Price: $£ 181$ 11s 9 d .
Automatic stereo switching with variable trigger level $(6-60 \mu \mathrm{~V})$; override mono switch and indicator; f.e.t. front end with a.f.c.; tuning meter and light aids; variablecapacitance diode tuning with pressbutton selection of up to six stations. Above details refer to f.m. section. Frequency coverage on a.m.: $145-350 \mathrm{kHz}$ (1.w.), $510-620 \mathrm{kHz}$ (m.w.), $3.15-8.8$ and $8.6-22.5 \mathrm{MHz}$. Grundig (Great Britain)

Ltd, 15 Orchard Street, London W1H 9AE.

Goodmans Stereomax
(a.m./f.m. stereo)


Sensitivity: $2 \mu \mathrm{~V}$ for 30 dB quieting. I.F. bandwidth: 300 kHz at 6 dB . Discriminator bandwidth: 600 kHz . A.M. rejection: 40 dB .

Channel separation: 37 dB at 1 kHz . Pilot tone suppression: 50 dB .
Aerial input: $300 \Omega$, balanced, $70 \Omega$ unbalanced.
Output voltage: 250 mV for $30 \%$ modulation.
Output impedance: $100 \mathrm{k} \Omega$.
Automatic stereo switching and stereo indicator; switched a.f.c. (pull-in range 100 kHz ); muting; tuning meter. Above details refer to f.m. section. Frequency coverage on a.m. $545-1650 \mathrm{kHz}$ (m.w.). External power socket for feeding other units. Goodmans Loudspeakers Ltd, Axiom Works, Lancelot Road, Wembley, Middx.

## Heathkit K/AJ-14 (f.m. stereo)

Sensitivity: $5 \mu \mathrm{~V}$.
Image rejection: 45 dB .
I.F. rejection: 80 dB .

Frequency response: $20-15000 \mathrm{~Hz}$ at 3dB (I.H.F.).
Aerial input: $300 \Omega$ balanced, $75 \Omega$ unbalanced.
Output voltage: 0.7 V for $1000 \mu \mathrm{~V}$ input. Output impedance: $20 \mathrm{k} \Omega$.
Channel separation: 30 dB at 1 kHz .
Price of kit: $£ 2418 \mathrm{~s}$, post and packing 5 s .
Mono/stereo switch and stereo indicator; a.f.c.; walnut or teak cabinet available. Heath (Gloucester) Ltd, Gloucester GL2 6EE.

Körting T500 (a.m./f.m. stereo)


Sensitivity: $3 \mu \mathrm{~V}$ for $26 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio at 12.5 kHz deviation.

Bandwidth: approximately 140 kHz .
Price: $£ 79$ 15s.
Automatic stereo switching with indicator; tuning meter; frequency coverage on a.m. $145-355 \mathrm{kHz}$ (l.w.), $510-1620 \mathrm{kHz}$ (m.w.) and $5.85-7.4 \mathrm{MHz}$. Special feature on a.m., automatic bandwidth ( $3-6 \mathrm{kHz}$ ) dependent on input signal strength. U.K. agents: Europa Electronics Ltd, Howard Place, Shelton, Stoke-on-Trent ST1 4NW.

## Leak Stereofetic (f.m. stereo)

Sensitivity: $2.5 \mu \mathrm{~V}$ for $30 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio.
Image rejection: 72 dB .
I.F. rejection: 80 dB .
A.M. suppression: 50 dB .

Aerial input: $75 \Omega$ unbalanced.
Output voltage: 0.9 V r.m.s. at 75 kHz deviation.
Output impedance: $200 \Omega$.
Channel separation: better than 35 dB at 1 kHz .
Price: $£ 68$ 1s 4d.
Switched a.f.c.; tuning indicator combined stereo indicator; f.e.t. front end and i.cs in i.f. stages and decoder; ceramic filter i.f. stages; automatic stereo switching with "mono lock" switch. Features "quasistereo", a method of progressively reducing noise while retaining some steren effect. H. J. Leak \& Co. Ltd, Bradford Road, Idle, Bradford, Yorks.

## L \& H "Signalmaster" 6087

(f.m., decoder optional)

Sensitivity: $2.5 \mu \mathrm{~V}$ for $20 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio.
Image rejection: better than 55 dB .
I.F. bandwidth: 250 kHz .

Output voltage: 200 mV (nominal).
Power supply: 9 V battery or 32 V external.
Price: 30 gn .
With decoder channel separation is better than 32 dB at 1 kHz ; a.f.c. switch; stereo indicator; available in teak or rosewood. Britimpex Ltd, 8/12 Rickett Street, London S.W.6.

## Nikko FAM-12F (a.m./f.m. stereo)



Sensitivity: $1.8 \mu \mathrm{~V}$ for 20 dB quieting. Image rejection: better than 45 dB at 1 MHz .
Channel separation: 40 dB at 1 kHz Output voltage: 0.5 V at $30 \%$ modulation. Price: $£ 688 \mathrm{~s}$ 3d.
Automatic stereo switching with indicator and mono override switch; tuning meter; switched a.f.c.; muting; noise filter; f.e.t.
front end. Above details refer to f.m. section. Frequency coverage on a.m.: $530-1605 \mathrm{kHz}$ (m.w.). U.K. agents: Howland-West Ltd, 2 Park End, South Hill Park, London N.W.3.

Pioneer TX-900 (a.m./f.m. stereo)


Sensitivity: $1.7 \mu \mathrm{~V}$ (I.H.F.).
Image rejection: 95 dB .
Selectivity: 65 dB .
$\mathrm{S} / \mathrm{N}$ ratio: 60 dB at $30 \%$ modulation.
Harmonic distortion: $0.3 \%$ at 400 Hz ,
$100 \%$ modulation.
Aerial input: $300 \Omega$ balanced.
Output voltage: 1 V at $400 \mathrm{~Hz}, 30 \%$ modulation adjustable on each channel.
Channel separation: 38 dB at 1 kHz .
Price: $£ 15418 \mathrm{~s} 3 \mathrm{~d}$.
Front end f.e.t; crystal filter i.f. stages; automatic stereo switching with mono override switch; adjustable stereo muting and interstation muting: switched a.f.c. Above details refer to f.m. section. Frequency coverage on a.m.: $\quad 525-1605 \mathrm{kHz}$ (m.w.). Shriro (U.K.) Ltd, Lynwood House, 24/32 Kilburn High Road, London N.W.6.

Philips RH691 (a.m./f.m. stereo)


Sensitivity: $7 \mu \mathrm{~V}$ for $26 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio at 15 kHz deviation.
Distortion: less than $1 \%$ at 75 kHz deviation.
Channel separation: 35 dB at 1 kHz .
Carrier suppression: 40 dB at 38 kHz
( 30 dB at 19 kHz ).
Audio response: $20-15000 \mathrm{~Hz} \pm 3 \mathrm{~dB}$.
Output voltage: 1.4 V at 40 kHz deviation.
Output impedance: $10 \mathrm{k} \Omega$.
Price: $£ 83$.
Switched a.f.c; automatic stereo switching with mono override switch and indicator; tuning meter; interstation muting. Above details refer to f.m. section. Frequency coverage on a.m.: 150 400 kHz (l.w.), $525-1604 \mathrm{kHz}$ (m.w.) and $5.9-18.2 \mathrm{MHz}$. Philips Electrical Ltd, Century House, Shaftesbury Avenue, London W.C.2.

Quad FM (stereo)


Sensitivity: $2 \mu \mathrm{~V}$ for 30 dB quieting.
Crosstalk: better than 30 dB at 1 kHz .
Suppression: better than 40 dB at 38 kHz .
Aerial input: $75 \Omega$.
Output voltage: 100 mV .
Output impedance: $100 \mathrm{k} \Omega$ each channel ( $50 \mathrm{k} \Omega$ mono).
Price: $£ 51$.
Automatic switching and stereo indicator with override manual switch; neon tuning indicator; a.f.c; fully tropicalized. Acoustical Manufacturing Co. Ltd, Huntingdon, Hunts.

## Radon 404 Mk2

(f.m., decoder optional).


Sensitivity: $15 \mu \mathrm{~V}$ (usable).
Bandwidth: 300 kHz at 3 dB . I.F. bandwidth: 170 kHz .
A.M. rejection: 26 dB for 20 mV input. Aerial input: $75 \Omega$.
Price: $£ 3918$ s with decoder fitted.
Switched a.f.c; permeability tuning. When decoder is fitted stereo switching is automatic with indicator. A Mark 3 version of this tuner has the stereo decoder fitted as standard. Radon Industrial Electronics Co. Ltd, Brooklands Trading Estate, Orme Road, Worthing, Sussex.

## Radford FMT. 3

(f.m., decoder optional)

Sensitivity: $2 \mu \mathrm{~V}$ for 30 dB quieting.
$\mathrm{S} / \mathrm{N}$ ratio: 70 dB .
Frequency response: $40-15000 \mathrm{~Hz}$ $\pm 1 \mathrm{~dB}$.
Harmonic distortion: less than $0.6 \%$ at 75 kHz deviation.
Detector bandwidth: 550 kHz .
Aerial input: $75 \Omega$ and $300 \Omega$.
A.M. suppression: 45 dB .

Output voltage: 2 V at 75 kHz deviation. Price: $£ 60$ plus p.t. (decoder fitted). With decoder, channel separation is better than 37 dB at 1 kHz ; carrier suppression better than 60 dB ; auto-
matic stereo switching with mono override switch; switched a.f.c; tuning meter; interstation muting; f.e.t. r.f. amplifier. Radford Audio Ltd, Ashton Vale Road, Bristol BS3 2HZ.

## Rogers Ravensbrook <br> (f.m. stereo)



Sensitivity: $5 \mu \mathrm{~V}$ (usable).
I.F. rejection: 85 dB .

Image rejection: 70 dB .
A.M. suppression: 50 dB .

Channel separation: better than 30 dB at 1 kHz .
Output voltage: 200 mV for $30 \%$ modulation.
Price: $£ 45$ plus case.
Front end f.e.t; integrated circuit i.f. strip; switched a.f.c; automatic stereo switching with indicator; tuning meter; interstation muting. Rogers Developments (Electronics) Ltd, 4-14 Barmeston Road, Catford, London S.E.6.

Rotel 120-ST (a.m./f.m. stereo)


Sensitivity: $2.5 \mu \mathrm{~V}$ for 20 dB quieting. Harmonic distortion: less than $1.5 \%$ at 1 kHz
Channel separation: better than 35 dB at $1 \mathrm{kHz} 100 \%$ modulation.
Output voltage: 1200 mV at $100 \%$
modulation.
Price: . £49 10s.
Automatic stereo switching with stereo indicator; a.f.c; tuning meter. Above details refer to f.m. Frequency coverage on a.m.: $535-1605 \mathrm{kHz}$ (m.w.). Distributors: Pullin Photographic Rank Aldis, P.O. Box 70, Great West Road, Brentford, Middx.

## Sony ST-5100

(a.m./f.m. stereo)

Sensitivity: $1.8 \mu \mathrm{~V}$ for $20 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio. Selectivity: 70dB (I.H.F.).

Image rejection: 90 dB .
Spurious rejection: 100 dB . A.M. suppression: 50 dB (I.H.F.). Frequency response: $20 \mathrm{~Hz}-15 \mathrm{kHz}$ $\pm 1 \mathrm{~dB}$.
Aerial input: $300 \Omega$ balanced,
$75 \Omega$ unbalanced.
Channel separation: better than 38 dB at 400 Hz .
Carrier suppression: 60 dB .
Price: $£ 99$ 15s.
Front end f.e.t.; i.f. filters; tuning indicators; a.f.c. control; muting switch. Above details refer to f.m. section. Frequency coverage on a.m.: $530-1605 \mathrm{kHz}$ (m.w.). Sony (U.K.) Ltd, 11 Ascot Road, Bedfont, Feltham, Middx.

## S.N.S. FMT/9 (f.m. mono)



Sensitivity: $10 \mu \mathrm{~V}$ for $30 \mathrm{~dB} \mathrm{~s} / \mathrm{n}$ ratio at 22.5 kHz deviation.

Limiting: $10 \mu \mathrm{~V}$ for full limiting.
Aerial input: 70-80 $\Omega$ unbalanced.
Output voltage: variable $0-500 \mathrm{mV}$.
Output impedance: $5 \mathrm{k} \Omega$.
Power supply: 9.1 V d.c. or optional a.c. mains unit.
Price: on application.
This tuner is available either for single programme reception or in switched version for up to four preset stations. It has a crystal-controlled oscillator and in the four-station version the above sensitivity figures are slightly impaired. Designed specially for radio distribution systems. S.N.S. Communications Ltd, 851 Ringwood Road, West Howe, Bournemouth BH11 8LN.

Sansui TU555 (a.m./f.m. stereo)


Sensitivity: $2 \mu \mathrm{~V}$ for 20 dB quieting. Image rejection: better than 50 dB . I.F. rejection: better than 60 dB . Channel separation: better than 35 dB . Aerial input: $300 \Omega$ balanced, $75 \Omega$ unbalanced.
Output voltage: more than 1.5 V .

Output impedance: greater than $10 \mathrm{k} \Omega$. Price: $£ 77$ 9s 2d.
Signal strength meter and stereo indicator; stabilized oscillator supply with no a.f.c; special noise cancelling circuit; f.e.t. front end. Above details refer to f.m. section. Frequency coverage on a.m.: $535-1605 \mathrm{kHz}$ (m.w.). U.K. importers: Brush Clevite Co. Ltd, Thornhill, Southampton SO9 1QX, Hants.

## Sugden R21 (f.m. stereo)



Sensitivity: $2 \mu \mathrm{~V}$ for 30 dB quieting. Frequency response: $30 \mathrm{~Hz}-15 \mathrm{kHz}$ $\pm 1 \mathrm{~dB}$.
I.F. rejection: 80 dB . Image rejection: 70 dB .
A.M. suppression: 50 dB .

Aerial input: $75 \Omega$ or $300 \Omega$.
Output voltage: 0.5 V .
Channel separation: better than 30 dB .
Price: approximately $£ 67$.
Front end f.e.t.; variable-capacitance diode tuning with four preset station buttons in addition to continuous tuning; switchable stereo filter giving low noise with reduced separation; special low-pass filter with 55 kHz cut-off; pilot tone and sub-carrier filters. Differently styled version (R51) available. J. E. Sugden \& Co. Ltd, Bradford Road, Cleckheaton, Yorks.

## Sinclair System 3000

This f.m. tuner will be released in late autumn. The only information available at the time of going to press is that sensitivity is expected to be $5-10 \mu \mathrm{~V}$ for 40 dB quieting. The circuit will incorporate a phase-lock loop discriminator, variable-capacitance diode tuning and an i.c. stereo decoder. Sinclair Radionics Ltd, 22 Newmarket Road, Cambridge CB5 8DU.

## Teleton STQ-201X (f.m. stereo)

Sensitivity: $2.5 \mu \mathrm{~V}$ for 20 dB quieting.
I.F. bandwidth: 240 kHz (3dB).

Image rejection: better than 50 dB .
$\mathrm{S} / \mathrm{N}$ ratio: 45 dB for 1 mV input.
Aerial input: $300 \Omega$ balanced.
Channel separation: 30 dB at 1 kHz .
Price: $£ 36$.
Stereo indicator; a.f.c.; tuning meter. Teleton Electro (U.K.) Co. Ltd, Teleton

House, Robjohns Road, Widford, Chelmsford, Essex.

Tripletone FM Mk2 (f.m. stereo)


Sensitivity: $2-\geqslant \mu \mathrm{V}$ for 20 dB quieting. Bandwidth: 210 kHz .
Aerial input: $70-80 \Omega$ unbalanced.
Output voltage: 0.1 V .
Channel separation: better than 30 dB at 1 kHz .
Price: $£ 37$ 19s 10d (teak case), $£ 35 \mathrm{ls} 3 \mathrm{~d}$ (chassis only).
Front end f.e.t.; a.f.c. (range 400 kHz ); automatic stereo switching and indicator. A mono version is available with provision for a plug-in decoder. The Tripletone Manufacturing Co. Ltd, 138 Kingston Road, Wimbledon, London S.W.19.

Trio KT-7000 (a.m./f.m. stereo)


Sensitivity: $1.5 \mu \mathrm{~V}$ (usable).
Frequency response: $20-15000 \mathrm{~Hz}$ -2 dB .
Harmonic distortion: less than 0.3\% (mono) at $400 \mathrm{~Hz}, 100 \%$ modulation. $\mathrm{S} / \mathrm{N}$ ratio: better than 70 dB at $30 \mu \mathrm{~V}$ input.
Image rejection: better than 100 dB at 100 MHz .
I.F. rejection: better than 100 dB .

Channel separation: better than 35 dB at 1 kHz .
Carrier suppression: better than 50 dB .
Aerial input: $300 \Omega$ balanced,
$75 \Omega$ unbalanced.
Output voltage: 1.5 V at $400 \mathrm{~Hz}, 100 \%$ modulation.
Output impedance: $7000 \Omega$.
Price: $£ 125$.
Three-f.e.ts front end; crystal filter and integrated circuit i.f. stages; signal strength meter and tuning meter; automatic stereo switching and indicator; interstation muting; step-type output level control. Above details refer to f.m. section. Frequency coverage on a.m.: $540-1600 \mathrm{kHz}$ (m.w.). U.K. agents: Lasky's Radio Ltd, 3-15 Cavell Street, Tower Hamlets, London E.1.

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Electronics, Television, Radio, Audio

Sixtieth year of publication


Our cover picture this month, which might be called "two kinds of digits", shows a five-by-seven array of light-emitting diodes made by Standard Telecommunications Laboratories. Display devices are discussed on page 444.

## IN OUR NEXT ISSUE

The first of a series of articles on the elements of linear i.cs

Constructional details of a 100 -watt quality amplifier

Review of some of the latest techniques in domestic sound and television receivers

September 1970
Volume 76 Number 1419

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## ibpa


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Ferrograph



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# Practical Aerial Handbook Gordon J . King, Assoc. IERE, MIPRE, MRTs. 

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## Ferrograph stereo amplifier F307

Ferrograph's F307 is one of the finest stereo amplifiers in the world. It has been designed to make the heart of great hi-fi systems.
It is an integrated stereo amplifier, built in the Ferrograph tradition to provide a unique combination of performance and facilities. Power output is 20 watts RMS per channel into a load of 8 ohms. Total harmonic distortion is less than $0.25 \%$ at 1 kHz at all levels up to its rated output. Silicon solid state devices are
used throughout, with F.E.T.'s in certain input stages to provide high input impedances and large overload margins and thus to accommodate a wide range of input sources, including tape, ceramic and magnetic pick-ups. radio and auxiliary inputs, at their optimum levels. The signal-tonoise ratio, measured with volume control at maximum, is better than 65 dB . Controls include four-input selector switch, switched mains outlets, press-button HF filter, comprehensive mono/stereo input
and output switching. The main controls are readily to hand on the front panels; all others are conveniently placed under a hinged flap.

In appearance, the F307 amplifier continues the uncluttered lines of the Ferrograph Series 7 recorder, the two making an ideal combination which is matched both visually and technically. But the amplifier is equally compatible with most other good recorders and hi-fi installations, suits innumerable
amateur and protessional uses, blends with any decor, stands attractively on any bookshelf or room-divider.
When planning your hi-fi system the F307 deserves your serious consideration. Your local Ferrograph specialist will be pleased to demonstrate it to you. Alternatively, please write or ring for details and address of nearest stockist. The Ferrograph Co. Ltd, The Hyde, Edgware Road Colindale, London NW9 Tel: 01-205 2241, Telex: 27774


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The IC-10 is primarily intended as a full performance high fidelity power and pre-amplifier, for which application it only requires the addition of such components as tone and volume controls and a battery or mains power supply. However, it is so designed that it may be used simply in many other applications including car radios, electronic organs, servo amplifiers (it is d.c. coupled throughout), etc. Once proven, the circuits can be produced with complete uniformity which enables us to give a full guarantee on every IC-10, knowing that every unit will work as perfectly as the original and do so for a lifetime.

## SPECIFICATIONS

Output: Frequency response: Total harmonic distortion: Load impedance:
ver gain: Supply voltage: Size:
Sensitivity: Input impedance:
atts R.M.S. continuous 5 Hz to $100 \mathrm{KHz} \pm 1 \mathrm{~dB}$ Less than $1 \%$ at full output. 3 to 15 ohms.
$110 \mathrm{~dB}(100,000,000,000$ times) total.
8 to 18 volts.
$1 \times 0.4 \times 0.2$ inches.
5 mV .
Adjustable externally up to 2.5 M ohms.

## CIRCUIT DESCRIPTION

The first three transistors are used in the pre-amp and the remaining 10 in the power amplifier. Class $A B$ output is used with closely controlled quiescent current which is independent of temperature. Generous negative feedback is used round both sections and the amplifier is completely free from crossover distortion at all supply voltages, making battery operation eminently satisfactory.

## APPLICATIONS

Each IC-10 is sold with a very comprehensive manual giving circuit and wiring diagrams for a large number of applications in addition to high fidelity. These include stabilised power supplies, oscillators, etc. The pre-amp section can be used as an R.F. or I.F. amplifier without any additional transistors.

## SINCLAIR <br> IC-10 <br> with IC-10 manual Post free.

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## Project 60



## Laboratory standard modular high fidelity

Sinclair Project 60 comprises a range of modules which connect together simply to form a compact stereo amplifier with really excellent performance. So good, in fact, that only 2 or 3 amplifiers in the world can compare in overall performance and now the constructor has choice of assemblies with either 20 or 40 watts output per channel, with or without filter facilities.
Themodules are: 1 . The $Z .30$ and $Z .50$ high gain power amplifiers. 2. The Stereo 60 preamplifier and control unit. 3. The Active Filter Unit. 4. 4 supply units-PZ.5; PZ.6; $P Z .7$ and PZ.8. In a normal domestic application, there will be no significant difference between PZ. 5 or PZ. 6 unless loudspeakers of very low efficiency are being used, in which case the PZ. 6 will be required. For assemblies using two $Z .50$ 's there is the PZ. 8 supply unit to ensure maximum performance from these amplifiers. No skill or experience are needed to build your system and the Project 60 manual gives all the instructions you can possibly want, clearly and concisely. Perhaps the greatest beauty of the system is that it is not only flexible now but will remain so in the future as new additions are made to the range. A stereo F.M. tuner is next to come. These and all other modules introduced will be compatible with those already available and may be added to your system at any time. And because Sinclair are the largest producers of constructor modules in Europe, Project 60 prices are remarkably low.

|  | System | The Units to use | In conjunction with | Your Project 60 Units will cost |
| :---: | :---: | :---: | :---: | :---: |
| A | Car Radio | 2.30 | Existing car radio, Sinclair Micromatic | 89/6 |
| 8 | Simple battery powered record player | 2.30 | Crystal pick-up, 12 V or more battery supply and volume control | 89/6 |
| C | Mains powered record player | Z.30 and PZ.5 | Crystal or ceramic P.U. Vol. control etc. | ¢9.9.0 |
| D | $20+20$ watts RMS stereo amplifier for most needs | Two Z.30s, Stereo 60 and PZ. 5 | Crystal, ceramic or magnetic P.U., most dynamic speakers, FM tuner, etc. | £23.18.0 |
| E | $20+20$ watts RMS stereo amplifier for use with low efficiency (high performance) speakers | Two Z.30s. Stereo 60 and PZ. 6 | High quality ceramic or mag. P.U., F.M. Tuner, Tape Deck, etc. All dynamic spkrs. | £26.18.0 |
| F | $40+40$ watts RMS deluxe stereo amplifier | Two Z.50s, Stereo $60 \mathrm{PZ}$.8 and mains transformer | As for E | £32.17.6 |
| G | Outdoor public address system | 2.50 | Microphone, up to 4 P.A. speakers, 12 V car battery with or without converter, controls | ¢5.9.6 |
| H | Indoor P.A | One Z.50, PZ. 8 and mains transformer | Mic., guitar, heavy duty speakers etc., controls | £17.8.6 |
| J | High pass and low pass filters | AFU | D, E or F as above | £5.19.6 |
| K | Stereo F.M. tuner | To ber | released shortly |  |

How to assemble and use Project 60 modules to best advantage in the above and other applications will be found in the fully descriptive Project 60 manual included with Project 60 systems. This 48 page manual is available separately, price $2 / 6 d$ including postage.
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## Z. 30 \& Z.50 POWER AMPLIFIERS

The Z.30 together with the $\mathbf{Z . 5 0}$ are both of advanced design using silicon epitaxial planar transistors to achieve unsurpassed standards of performance. Total harmonic distortion is an incredibly low $0.02 \%$ at full output and all lower outputs. Whether you use the Z.30 or $Z .50$ power amplifiers in your Project 60 system will depend on personal preference, but they are the same physical size and may be used with other units in the Project 60 range equally well. For operating from mains, for the $Z .30$ use PZ. 5 for most domestic requirements, or PZ. 6 if you have very low efficiency loudspeakers. For $\mathbf{Z . 5 0}$, use the PZ.8 described below.

## SPECIFICATIONS $\mathbf{2} .50$ units are inter-

 changeable with 2.30 s in all applications. Power OutputsZ. 3015 watts R.M.S. into 8 ohms, using $35 \mathrm{~V}: 20$ watts R.M.S. into 3 ohms using 30 volts.
Z. 5040 watts R.M.S. into 3 ohms from 40 volts 30 watts R.M.S into 8 ohms, using 50 volts. Frequency response 30 to $300,000 \mathrm{~Hz} \pm 1 \mathrm{~dB}$ Distortion $0.02 \%$ into 8 ohms
Signal to noise ratio better than 70 dB unweighted Input sensitivity 250 mV into 100 Kohms For speakers from 3 to 15 ohms impedance Size $3 \frac{1}{2} \times 2 \frac{1}{4} \times \frac{1}{2}$ ins.

Curve shows power versus distortion for 2.30 and 2.50

## STEREO 60 Pre amp/Control Unit

Designed for the Project 60 range but suitable for use with any high quality power amplifier. Again silicon epitaxial planar transistors are used throughout, achieving a really high signal-to-noise ratio and excellent racking between channels. Input selection is by means of push buttons and accurate equalisation is provided for all the usual inputs. SPECIFICATIONS

- Input sensitivities - Radio - up to 3 mV . Mag. p.u. - 3 mV : correct to R.I.A.A. curve $\pm 1 \mathrm{~dB}: \mathbf{2 0}$ to $25,000 \mathrm{~Hz}$. Ceramic p.u. -- up to 3 mV : Aux. up to 3 mV .
- Output -250 mV .
- Signal-to-noise ratio - better than 70 dB
- Channel matching - within 1 dB .
- Tone controls - TREBLE +15 to -15 dB at 10 kHz : BASS +15 to -15 dB at 100 Hz .
- Front panel - brushed aluminium with black knobs and controls.
- Size $8 \frac{1}{d} \times 1 \frac{1}{2} \times 4$ ins.

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Curve to show bass and treble cut and boost.

## ACTIVE FILTER UNIT

For use between Stereo 60 unit and two 2.30 s or $\mathbf{Z . 5 0}$ s, the Active Filter Unit matches the Stereo 60 in styling and is as easily mounted It is unique in that the cut-off frequencies are continuously variable, and as attenuation in the rejected band is rapid ( $12 \mathrm{~dB} /$ octave). there is less loss of the wanted signal than has previously been possible. Amplitude and phase distortion are negligible. The Sinclair A.F.U. is suitable also for use with any other amplifier system.

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 and guaranteed

## POWER SUPPLY UNITS

The units below are designed specially for use with the Project 60 system of your choice Illusiration shows PZ. 5 power supply unit to left and PZ. (for use with Z.50s) to the right. Use PZ. 5 for normal $\mathrm{Z}$..30 assemblies and PZ. 6 where a stabilised supply is essential.
$\mathrm{PZ}-530$ volts unstabilised $£ 4.19 .6 \quad \mathrm{PZ}-845$ volts stabilised (less mains transformers) $£ 5.19 .6$ PZ-6 35 volts stabilised $£ 7.19 .6 \quad$ PZ-8 mains transformer $£ 5.19 .6$

## GUARANTEE

If within 3 months of purchasing Project 60 modules directly from us, you are dissatisfied with them, we will refund your money at once. Each module is guaranteed to work perfectly and should any defect arise in normal use we will service it at once and without any cost to you whatsoever provided that it is returned to us within 2 years of the purchase date. There will be a small charge for service thereafter. No charge for postage by surface mail. Air-mail charged at cost.


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| Model 360-Th | ¢7 17 | 6 | Model 380-CE | f15 | 2 | 6 |
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This new meter kit by TMK offers the professional, electronics hobbyist and student the unique opportunity of building a really first class precision mutimeter at a worth while saving in cost. The impactresistant bakelite cabinet is supplied with the meter scale and movement mounted in position. The highest quality in components and $\mathbf{1 \%}$ tolerance resistors are used throughout. Supplied complate in
MODEL 5025 5.0.000.e.,. EEATuAING
A highly reliable Instrument using an entirely new range selection mechanism which permits the use of a really large meter In a more compact cabinet. The range selected is clearly indicated on the actual meter face facilitating instant identifcation without taking your eyes from the meter. High speed overload protection circuit. Special A and MA measurement ranges
SPECIFICATION: SPECIFICATION:

- DCV: 0.0.25-2.5-10-50-250-1,000V at $25 \mathrm{~K} / \mathrm{OPV} 0-0.125-1.25-$ - ACV: $0.3-10-50-250-1,000 \mathrm{~V}$

500 V at 5 K 10 PV .

- DC $\mu \mathrm{A}: 0-25 \mu \mathrm{~A}$ at $125 \mathrm{~mA}: 0-50 \mu \mathrm{~A}$ at 250 mA
-DCmA: 0-2 5-25-250mA at 125 mV . 0-5-50-500mA 250 mV - DC Amps: $0-5 A$ at $125 \mathrm{mV}: 0-10 A$ at 250 mV .

Resistance: $0-10 \mathrm{M} / \mathrm{ohms}(13,85,650.6 .5 \mathrm{~K}$ and $65 \mathrm{~K} / \mathrm{ohms}$ at centre scale).

- Output Capacilor ( $0.1 \mu \mathrm{~F}, 400 \mathrm{~V}$ w) in serles with ACV ranges - Decibels:- 20 to +81.5 dB in 10 ranges.
cabinet, size $5 \frac{1}{4} \times 6 \frac{1}{a} \times 2 \frac{7}{5} \mathrm{in}$. Sirang restilent plastic handle. Complete with test leads.


## KIT PRICE $£ 10: 10.0$

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ALSO AVAILABLE READY-BUILT AND TESTED E12.10.0. Post $5 /-$

Also available. TMK Model 200 Meter 20,000 ohms/N 92/-. Instructions and data available before purchase-Send SAE plus 2/6. Refundable if you purchase Kit.


## LASKYS MODEL TM5

Another new look pocket multi-meter from Lasky's providing case-size and value. The "slimline" impact resistant 2 zin. square meter. Readability is superior on all low ranges: making this an excellent instrument for servicing transistorised equipment. Mecessed click stop selection switch. Ohms zero adjustment. Buff finish with crystal clear meter cover

- DC/N: 3-15-150-300-1,200 at 5K ohms/V - $A C / \mathrm{N}: 6-30-300-600$ at $\mathbf{2 . 5 K}$ ohms $/ \mathrm{V}$
- ACN:6-30-300-600 at 2.5K oh
- Resistance: $0-10 \mathrm{~K}$ ohms, 0-1 M ohms
- Decibels: - 10 dB to 16 dB
- Complete with test leads, battery and instructions

LASKYS PRICE 49/6 P. \& P. 2/6

## LASKYS

## TM1

The first of Lasky's new-look top value meters, the TM-1 is a really tiny pocket multimeter providing "big" meter accuracy and performance. Precision movement calibrated $t 0 \pm 3 \%$ of full scale. Click stop range selection switch. Beautifully designed and made impact resistant black cas

DC/V: 0-10-50-250-1000 at 1 K ohms $/ \mathrm{N}$

- AC/V : 0-10-50-250-1000 at 1K ohms/V
- DC CURRENT: $0.1 \mathrm{~mA}, 100 \mathrm{~mA}$.
- Resistance: 0-150K ohms
- Decibels: $-10+22 \mathrm{~dB}$
- Complete with test leads, battery and instructions

Size Only $3 \frac{1}{4} \mathrm{in} . \times 2 \frac{3}{8} \mathrm{in} . \times 1 \frac{1}{4} \mathrm{in}$.


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Measuring $17 \frac{1}{2}$ " $10_{4}^{3 \prime \prime} \times 6_{4}^{3 / \prime}$. the Duo type 2 speakers are beautifully finished in teak veneer with matching vynair grills. They incorporate a $10_{2}^{1 " n} \quad 6 \frac{11}{4}$ " drive unit and high frequency speaker, both of which are of 3 ohms impedance. The Duo speaker system is also available separately at £6.6.0. each plus 15$)^{\prime}-P$ \& $P$. Complete stereo system £41 plus E2.10 P \& P.

High fidelity transistor stereo amplifier employing field effect transistors, With this feature \& accompanying guaranteed specifications below, the Viscount F.E.T. vastly F.E.T. MK \| E14.5s. plus $7 / 6$ P. \& P. surpasses amplifiers costing far more.

## Size: $12 \frac{1}{2}^{\prime \prime} \times 6^{\prime \prime} \times 2 \frac{3{ }^{\prime \prime}}{}$ in teak-finished case.

Specification: Output per channel 10 watts r.m.s. Frequency bandwidth 20 Hz to $20 \mathrm{kHz} \pm 1 \mathrm{~dB}$ (e) 1 watt.

Total distortion: @ 1 kHz @ 9 watts $0.5 \%$.
Input sensitivities: CER, P.U. 100 mV into 3 meg ohms. Tuner 100 mV into 100 K ohms.
Tape 100 mV into 100 K ohms.

Overload Factor: Better than 26 dB .
Signal to noise ratio: 70 dB on all inputs (with vol. max). Controls: 6 position selector switch ( 3 pos. stereo $\&$ 3 pos. mono). Separate Vol. controls for left \& right channels. Bass $\pm 14 \mathrm{~dB}$ @ 60 Hz . Treble (with D.P.S. on/off) $\pm 12 \mathrm{~dB}$ @ 10 kHz . Tape Recording output sockets on each channel.

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Mk II (MAG. P.U.) £15.15.0 plus $10 \%$ - \& p Specification same as Mk. I. but with the following inputs.
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(Type 2) $28 \mathrm{r} . \mathrm{p} . \mathrm{m}$. torque 20 lb in
reversible $1 / 80$ th h.p. 50 cycle .28 amp.
The above two precision made U.S.A. motors are offered in 'as new' condition. Input voltage of motor 115 v A.C. Supplied complete with transformer for $230 / 240 \mathrm{v}$ A.C. input
Price, either type $£ 3.3 .0$ plus $6 / 6$ P. \& P. or less transformer E2.2.6 plus 4/6. P. \& P.
These motors are ideal for rotating zerials, drawing
curtains, display stands, vending machines etc. et

## $230 / 240 \mathrm{~V} 10$ RPM MOTOR

(Non Reversible)
Extremely powerful. Con tinuously rated. Offered at the low price of $35 /=$ pose paid



POWER RHEOSTATS
(NEW) Ceramic construction, windEnamel, heavy duty brush assembly designed for tontinuous duty. AVAILABLE FROM STOCK IN THE FOLLOWING II VALUES: 100 WATT I ohm $10 \mathrm{a}, 5$ ohm 4.7 a ., 10 ohm 3a., 25 ohm 2 a ., 50 ohm l.4a., 100 ohm la., 250 ohm $-7 \mathrm{a} ., 500$ ohm 45 a ., I k ohm 280 mA ., I. 5 k ohm m
$230 \mathrm{~mA}, 25 \mathrm{k}$ ohm $-2 \mathrm{a} ., 5 \mathrm{k}$ ohm 140 mA ., Diameter $230 \mathrm{~mA} ., 2 \cdot 5 \mathrm{k}$ ohm 2 aa .5 k ohm 140 mA ., Diameter 3 tin. Shaft length $\frac{1}{2} \mathrm{in}$. dia. ${ }^{15} 5 \mathrm{in}$., 27/6. P. \& P. I/6.
50 WATT $1 / 5 / 10 / 25 / 50 / 100 / 250 / 500 / 1 \mathrm{~K} / \mathrm{I} \cdot 5 \mathrm{~K} / 2 \cdot 5 \mathrm{~K} /$ 50 WATT $1 / 5 / 10 / 25 / 50 / 100 / 250 /$ 5 K ohm. All at $21 / \mathrm{F}, \mathrm{P}$. \& P. $1 / 6$.
$25 \mathrm{WATT} 10 / 25 / 50 / 100 / 250 / 500 / 1 \mathrm{~K} / 1 \cdot 5 \mathrm{~K} / 2 \cdot 5 \mathrm{~K}$ ohm. All at $14 / 6$, P. \& P. $1 / 6$.
Black Silver Skirted knob calibrated in Nos, 1-9. 12 in. dia. brass bush. Ideal for above Rheostats, $3 / 6$ each

MOTOROLA MACII/6 PLASTIC TRIAC 400 PIV 8 AMP
Now available EX STOCK supplied complete with fult data and applleatlons sheet. Price 21/- plus $1 / 6$ P. \& P. चै.M.c. ILLUMINATED
LATCHING PUSH BUTTON KEY SWITCH No. S525594 LOCK $4 \mathrm{c} / \mathrm{o}$
Complete with mounting Gracket, P ush Knoband Lenses

- state colour preferencel. PRICE $19 / 6$ each excluding bulb, Post Paid. Discount for quantities of 200 excluding


## STRODELSRPDELSTRODEL




## ELECTRONIC ORGAN KIT


deal present for Elec tronically minded boy. Easy to build, solid
state. Two fuil octaves (less sharps and flats) (less sharps and flats).
Fitted hardwood case using two penlite $1 \frac{1}{2} v$. batteries. Complete set of parts including speaker, etc., together with full instructions and functional, inseructive gift for any boy or girl. Price 63.0.0. P. \& P. 4/6.

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50 easy to build Projects. No soldering, no special tools required. The Kic includes Speaker, meter, Relay,
Transformer, plus a host of other components and a $56-$ Transformer, plus a host of other components and a Projects are: Sound level Meter, 2 Transistor Radio, Amplifier etc., etc. Price 67.15.0. P. \& P. 6/-.

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10 easy to build Projects including: Radio, Morse Oscillator, L F Oscillator ete. A Solar Cell is included in this Kit as alternative power for some of the circuits also a 14 -page step by step instruction leaflet. Price $\mathbf{\$ 3 . 1 7 . 6 .}$

25 ohm coil, 24 V. D.C. ope
$\mathbf{5 5 . 1 7 . 6 \text { , plus } 2 / 6 \text { P. \& P. }}$
6 BANK 25 WAY FULL
WIPER 25 ohm coil, 24 v. D. operation. 6610.0 plus 216 P \& 8-BANK 25-WAY FULL WIPER 24 v. D.C. operation, 87.12 .6 , plus 4/-P. \&

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NEW SIEMENS PLESSEY,
MINIATURE RELAYS AT A
HIGHLY COMPETITIVE PRICE.
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## MINIATURE RELAYS

9-12 volt D.C. operation. 2 e/o 500 M. A. contacts. Size only lin. $x \frac{1}{8} \times \frac{1}{2}$ in. Price $11 / 6$ Post paid.
 SPECIAL OFFER
Relay 18124 v. D.C. 2 c/l ${ }^{3}$ Amp contacts.
400 ohm coil. NEW. $9 / 6$ P. \& P. $1 / 6$ or 400 ohm coil. NEU,
3 for $30 /-$ post paid.
TYPE A.G.C. 1 M 1812 V . A.C. ${ }^{3}$ amp contacts.
NEW $9 / 6+1 / 6$ p. \& P. or 3 for $30 /$.

RECHARGEABLE NICKEL CAD. BUTTON CELLS
 rate, complete with 200/250
unused. Price $9 / 5$ each plus
unuse. Price
units for E 1
post
paid.
V.

C̄OMPLETE NI. CAD. BATTERYOUT. FIT (EX W.D.)
2 metal carrying cases
each containing $10 \times 1.2$ each containing $10 \times 1.2$
volt $7 A H$ (12v) batteries. also $10 \times 1.2 v 22 \mathrm{AH}$
( 12 z ) batreries ( 40 bat(12v) batteries ( 40 batvoltage, dual meter,
thyristor controlled
 charging unit. Designed
for charging the 7 AH taneously. $100-250 v$ AC. Builtage can be adjusted between power supply for field mork try specification. Ideal makers price. 2 sets of batteries, I charging unit. The set 45 c c. \& p. $30 /-$.

## NICKEL CADMIUM BATTERY

1.2 v. 35 AH. Size $8 \frac{1}{}$ high $\times 3 \times 1+$. $30 /-$ each, plus $1 /-$ $P$ \& \& $P$
Sintered Cadmium Type 1.2 v. 7AH. Size: height $3 \frac{1}{2}$ in., width 2 lin . $X 1 \frac{1}{\text { In in }}$. Weight: approx 13 ozs ExTested 12/6. P. \& P. 2/6.

## NEW MODEL HIGH FREQUENCY

 TRANSISTORISED MORSE OSCILLATOR Adjus table tone tontrol. Fitted with moving eoil speaker, also earpiece for personal monitoring. Complete with morse key. 45/-plus 3/6d. p. \& p.SEMI-AUTOMATIC "BUG" SUPER SPEED
MORSE KEY
7 adjustments, precision tooled,
speed adjustable 10 w p.m. to as
high as desired. Weight $2 \frac{1}{2} l \mathrm{lb}$. E $4 / 12 / 5$ post paid.


INSULATED TERMINAL8 Available in black, red, white yellow, blue and green. New

Ex. W.D. MINIATURE BLOWER UNIT 18-24 v. D.C. operation, overall length P. \& P. $2 / 6$.

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MINIRACK MULTICHANNEL
OSCILLOGRAPH. MUR 12

 Cosor. Model 1431. Complete with
motor, auto tranatormer and capacitor untt. Price. ....E49.10.0 plus aurringe
 As illustrated.
Price
Prinated. head io exit 10.0 plus carriage Viewing head to suit Type 'A' camera.
Prico.......... $\mathbf{~ £ 2 5 . 1 0 . 0 ~ p l u s ~ c a r r i a g e ~}$

## VOLSTATS

| OLype |  |  |  |  |  |
| :---: | :---: | :---: | :---: | :---: | :---: |
| creme | ${ }_{190}^{190 / 280}$ |  |  | W. |  |
| MT 161E |  |  | 12 | w. |  |
| MTZ 161 A | 190/260 | 50 | 30 | 50 w . |  |
| CV 800 | 951130 | 0 | 5 | Atw |  |
| $\mathrm{CV}_{\mathrm{CV}} \mathrm{soj}$ | 190,280 | 50 | ${ }_{230}^{230}$ | ${ }_{150}^{50}$ |  |
| CV 150 | 110 | ${ }_{80}$ | ${ }_{230}$ | ${ }_{250}^{150} \mathrm{~W}$. |  |
| MT 16 | 190/260 | 4 | 230 | 50 W . |  |
| MT 14 | 190/2 |  | 230 | ${ }_{500} 150 \mathrm{~W}$ |  |
| M | 190 | ${ }_{50}$ | 230 | 500 150 |  |
| ${ }_{4 T} 202 \mathrm{~A}$ | 190/260 | b0 | 230 | 500 |  |
| $30 \mathrm{MB7790}$ CVH coid | 210/250 | S0 | - |  | ${ }_{\text {c10 }} 10.10$ |
|  |  | 50 | 40 |  |  |
| A | 19 | 80 | 240 | 1000 W. |  |

GALVANOMETERS (PENCIL TYPE) SPECILow Frequency Types
Type No.

|  | Prequeney Resporse $\pm 5 \% \mathrm{c} / \mathrm{s}$ | Terminal Resistance in Oh7ns | sensitivity for <br> a 3 sem optical <br> polh MA/cm |  |
| :---: | :---: | :---: | :---: | :---: |
| EB/20 | 20 | 85 | 0.4 Micro $\mathrm{A} / \mathrm{cm}$ | 233 |
| EB/35 | 35 | ${ }^{75}$ | 0.67 Micro $\mathrm{N} / \mathrm{cm}$ | 233 |
| EB/40 | 40 | 95 | 0.43 Micro A/cm | 33 |
| EB/400 | 40 | 45 | 2.1 Micro $\mathbf{A} / \mathrm{cm}$ | \&33 |
| EB/60 | 60 | 90 | 0.7 Miero A cm | ${ }^{\text {¢ }} 33$ |
| EB 100c | 100 | 60 | 9.1 Miero A cm | E33 |
| EB, 100 | 100 | 75 | $2.7 \mathrm{Micros} \mathrm{A} / \mathrm{cm}$ | 233 |
| EB/160 | 160 | 70 | $5 \mathrm{Micron} \mathrm{A} / \mathrm{cm}$ | 833 |
| EBB/200 | 200 | 70 | 21 Micro A cm | ع33 |
| EB/300 | 300 | 120 | ${ }_{25} 2$ Micro Alcm |  |
| EB/450 | 450 | 120 | 50 Micro A/cm | c33 |
| Hiibh Preod | Typen |  |  |  |
|  | 1,000 |  | $0.46 \mathrm{MA} / \mathrm{cm}$ | 833 |
| EBIII,600 | 1,600 | 85 | $0.9 \mathrm{MA/cm}$ |  |
| EB $/ 2,200$ | 2.200 | 85 | $1.9 \mathrm{MA/cm}$ |  |
| EB/ $/ 2,500$ | 2,500 | 42 | $4.8 \mathrm{MA} / \mathrm{cm}$ |  |
| EB/3,300 | 2.300 | 45 | 6. 3 M $\mathrm{M} / \mathrm{cm}$ |  |
| EB/4,000 | 4,000 | 45 | 7.2 M A/em |  |
| EB/3,000 | 8,000 | 45 | $13.3 \mathrm{ma} / \mathrm{cm}$ | 233 |
| KBB/8,000 | 8,000 | 45 | $22 \mathrm{MA} / \mathrm{cm}$ | ${ }^{2} 33$ |
| EB/10,000 | 10,000 | 45 | ${ }_{8}^{28} \mathrm{MA} / \mathrm{cm}$ |  |
| EB/20,000 | 20,000 | 90 | $85 \mathrm{MA} / \mathrm{cm}$ | C50 |

DIGITAL VOLTMETERS

DM2004. For DC measurement from 1 mV to I kV Sale 1999 in two manually selected stages of 0-999 and 00-1999. Input impedance Range I: IM ohms;-Ranges 2, 3 and 4: IOM ohms. Aceuracy $0.1 \%$ of reading.

DM2010. Scale 109999. For DC. measurement of 10 microvolt to 1.1 K volt. Input $Z$ greater than 25000 M ohms. Accuracy $0.001 \%$ F.S.D. C.M.R. DC 160 dB . Parallel B.C.D. output (not isolated). ........ Price 6500 LM902.2. Seale 1599 in 7 ranges from 0.IV to $1,000 \mathrm{~V}$. Input $\mathrm{Z} 0-1,000 \mathrm{~V} 100 \mathrm{M}$ ohms. Accuracy $0.5 \%$. Print out facility two 50 -way sockets for Printer or remote display. 6 V DC 300 mA maximum combined outpue.

LM1420.2. For DC measurement from $01-1,000 \mathrm{~V}$ in 6 Ranges. Input $Z$ not less than $10 M$ ohms. Accuracy $0.05 \%$ of Indication, Calibration. Internal Weston Cell. C.M.R. greater than 150 dB . Can be used as a counter or as a simple stop watch or to determine the frequency Price 6300

DM2020. Scale 19999, 10 microvolt resolutions. Accur acy $0.01 \%$. B.C.D. output. . . . . . . . . . . . . . . . . Price $\S 325$

DM2001. Scale 19995. DC. Accuracy 0.05\%. Range 50 microvolt to 2 kV . $1 / \mathrm{P}$ impedance greater than $10,000 \mathrm{M}$ ohms. Parallel B.C.D. output or Decimal (not isolated).

AC-DC CONVERTERS TYPE $2140 /$ Al-BI and 2140/A3-83
A flexible modular system for use with a DVM for accurate mean (RMS) or true (RMS) Voltage measurements, Module AI LF Amplifier $\times 0.1$ to $\times 1,000$. Module A3 LF Amplifier $\times 0.1$ to $\times 100$
2140/AI-BI 1,000V True RMS Converter................ . . .
2140/A3-B3 200V Mean (RMS CALIBRATED) Converter.
Price C 150

(No. 5) IMPEDANCE BRIDGE TYPE TF936
 volts monitored and varisbles. Automatic detector sensitivity control. Rugged pan-climatic construction.
Measures 1 , from 1 microll to 100H. 0 Mrora 1 pF to 100 malerof and re sistance from 0.1 ohm to 10 M ohm
Price.......... 805 carriage extra

## MOTORS

HIGH PRECISION MAINS $230 \mathrm{~V} 50 \mathrm{~Hz} 1 / 8 \mathrm{~h} . \mathrm{p}$. continuonsly ratod 3000 r.p.m. Made by Groydon Engineer.
ing. Model KA Bo $\mathbf{N F B}^{\text {. Sulinable for }}$ ing. Model KA 60 JFB . Suing ble for
capsitan motor. size 8 in . long, 4it in capsinan moror. 8 ize 8 in. long, $4 t$ in
dlameter with 6 in . dismeter fange and 4 fixing hotes. f4/10/0 each. P, \& P. $25 /$ -


LOW TORQUE HYSTERESIS MOTOR MA2J Ideal for instrument chart drives. Extremely quilet, aseful in areas
where ambient noise levels are low. High starting torque enable relative high inertia loads to be driven up, to $6-02 / \mathrm{in}$. Available in


 1/80 r.p.m... $1 / 120$ r.p.m., $1 / 240$ r.p.p.
$1 / 440$ r.p.m. $25 /=$ each. P. \& 8 P. $3 /$.

HYSTERESIS REVERSIBLE MOTOR
Incorporating two coila, Each coll when energised will produce opposite rotation of output shaft. 240 V 50 Hz . \& R.p.m., i r.p.nı.
$1 / 6 \mathrm{r}$. p.m., $120 \mathrm{~V} 60 \mathrm{~Hz}, 1 / 10 \mathrm{r} . \mathrm{p} . \mathrm{m} ., 30 /=$ each. P. © P. $3 /=$.

SYNCHRONOUS MOTORS.
Model \& 71 r.p. h. and $1 / 60$ r.p.h. self otarting complete with gearing Equipment. $40 \%$ P. \& P. $3 /$.

DATA TRANSMISSION-SYNCHROS
A selection from our wide range
Torque Recelver
Tonque Recelver 11TR4a sperry
$\begin{array}{lll} \\ \text { ACN } 1550 \text { Sperry } & 90 / 115 \mathrm{v} & 400 \\ & 26,12.3 & 400\end{array}$
Torque Receiver 11 TR 4 a Pullin
Control Tranaformer 11CT4A Muirthead ControlTransformer 11CT4a Control Tranaformer 11CT4a Control Tranaformer 11CX 48 Torque Tranamitter ACA/AE Torque Tranamitter 11MD3 Bperry
Pullin Pullin
Ketay
8mith Ketay
8mith
Muirhead Muirhead
Muirhead $\qquad$ $\begin{array}{ll}1 / 115 \mathrm{v} & 400 \\ 6 \mathrm{v} & 40 \\ 0 \mathrm{v} & 40 \\ 28 \mathrm{v} & 40 \\ 115 / 90 \mathrm{v} & 400 \\ 11 / 990 \mathrm{v} & 400 \\ 26 \mathrm{v} & \\ 115 / 00 \mathrm{v} & 4\end{array}$ 118/90v 400
CARRIAGR

## EYERSHED \& VIGNOLES

SPLIT FIELD SERVO MOTOR

SYNCHRONOUS MOTOR WITH GEARBOX Motor 11 M83 kearbor type 11 H 21 . This unit is an 8000 r.p.m., $116 \mathrm{v}_{\mathrm{m}}$ $9.92 / 1$. Motor torgma 602. in. length c/w gearboz $25 / 8 \mathrm{ln} . \times 1$ of diameter.

RAGONOT MOTOR
28PM 3 -phase $50 \mathrm{~Hz} 1 / 20 \mathrm{HP}, 1500$ DRIVES Rotor movea I in axially "Bwitch on" to take up drive and on 8witch of
odisengage drive. $45 /=$ each. P. © P. P. $10 / 2$

## GENERATORS

## AVO SIGNAL

GENERATOR CT 378
mentals up to 450 MHz on H Funda Scale calibration accuracy $\pm 1 \%$. continuously variable into 75 ohm 1 mikerc volt to 12.5 mV into 50 ohm using fixed attentuator pad. Hodula
tion facilities. A/F o/p facility. 0 / evel meter. Force o/p facllity. Bize



OSCILLATORS \& SIGNAL GENERATORS (I
 (T104) NEW AUTOMATLC CYCLIMG Osculator. Acos 1. Mains supply... (I108) LOW FREQUENCY DECADE OSCILLATOR D-8ab-A Max. O/p 1 W in $600 \Omega$ above 30 Hz ....................... Price 845 (H09) DECADE O8CLLLATOR D-850-B. Range $1 \mathrm{~Hz}-111 \mathrm{KHz}$ Price 2 \& (I110) L.P. OsCILLATOR a 420 FURZEHILL. Range 1.4 Hzs HONTKOR-SMTHLATOR AND AUTOMATIC FREQUENCY (H.
 (149) GADGE OSCLLLATOR M 700L SOUTHERM DISTRUMENTB. (I18 sional Genergator crenc. Range $85-30$ MHz. O/p. (I15) AUDIO FREQUEMCY GEMERATOR. Type JR. ADVANCE. ...........rice 2 . ( 183 ) gIGNAL aENERATOR CT 480 SAMDERS. Range 7 KHz -
$12 \mathrm{KHz}, \mathrm{O} / \mathrm{p}$. $0= \pm 60 \mathrm{~V}$. Attenuation range -10 to +100 dB .
(79) WOBULATOR aM $2877 / 02$ PBTLLIP8 .. Price $£ 65$ (I42) NOISE GENERATOR CT 410 WAYNE KERR. Frequency
 FM/AM SIGNAL GENERATOR. TYpe 8G. G3D. ADVANCE. Range FM deviation $\pm 100 \mathrm{~K} \mathrm{~K}_{2}, \ldots \ldots . . . . . . .$. (I105) STONAL GENERATOR Mod. B8A TAYLOR. Range 100

D.C. TACHOGENERATOR Type dia $3 / 16 \mathrm{in} 3 / 8$ in lo.m. Drive £16/10/0.

A.C. MOTOR GENERATOR

Type G1005 Motor 8pec, 6000 r.p.m. Torque $25 \mathrm{grn} / \mathrm{cmn}$. Control
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## 49-53 PANCRAS ROAD, LONDON, N.W.I. Tel: 01-837 7781/2. Cables: SELELECTRO

MEASURING INSTRUMENTS AND RECORDERS

(R3) SNGLE PEN, DC MILLIAMMETER. 0-1mA. Chart width
 (R4) SINGLE PEN. DC MILLIAMMETER, $0-1 \mathrm{~mA}$ or $0-500$ micro amp. Chart width 3 in . 8 peed 1 ln . sind 6 in ./hr. Fitted alarn ( $0-500$ micro A). Malns power supply.............. Price $£ 48.10 .0$ (R24) Sinole Pen. dC Milliammeter. 0.2 mA , Chart widh 4 in . Speed 1 in . and $6 \mathrm{im} . / \mathrm{hr}$. and 1 in . and $6 \mathrm{im} / \mathrm{minn}$. Clock work P9) PEN DC MICLAMMETER $0-15 \mathrm{~mA}$. Chart width 8 In peed 6 in. and 12 in./hr. Mains supply................... Price \&75 (R9) UNIVERSAL MOLTIPONNT. 1.24 point suitable quantities with slow rate of change. Chart width 12 in . Bpeed: 3 ranges, 61
ratlo. Sensitivity $0.100^{\circ} \mathrm{C}$ based on 0.75 mV FSD using Thermocouple pick up.............................................. Tidth 64 in Speed: 20 and 720 min. fhr. Also available 0.100 $0-400^{\circ} \mathrm{C}$ using Thermocouple pick ups............ Price $₹ 79.10 .0$ (RII) CAMBRIDAE TEMPERATURE RECORDER SINGLE PEN. Circular Scale. Uses ether bulb and capillary tube. Range:
$50-300^{\circ} \mathrm{C}$. Chart dia. 108 in. ( $24-\mathrm{hr}$. markings). Maing supply... \&45 (R18) MERSTED TEMPERATURE RECORDER. Two Pen $200^{\circ} \mathrm{C}$, c/w bulbs and capillary tublag. Mains supply, 24 hr . Cha (R18) FIDDEN Mk, II SERVOGRAPE, single point fitted with urret head to enable converaion to 4 point. User epacitlve sensin. nput. Chart dia. 11 in. Speed: 1 rev.ha. seasilivis 50 micro Amp R1e) KENT Mk. II SWGLE POINT, Chart width $94 \mathrm{in}$. . Bpeeds r.e. $0-600^{\circ} \mathrm{C}, 0-1,000^{\circ} \mathrm{C},-50$ to $-200^{\circ} \mathrm{C}, 0-100^{\circ} \mathrm{C}$. Also available multipoint. General purpose slow responge suitable Temperature Humidity, etc. Response s. secs. for F8D. Supply. Price 84910 (R25) SINGLE PEN. DC MILLIAMMETER, 0-1mA. Chart Fidth RE7) SINGLE PEN DC MILIIAMMETER $15-0-5 \mathrm{~mA}$. OH damped movement. Chart width 7 in. Bpeed: 1 in./hr. Clockwork drive
B-day. Terminal Resistance 100 ohms................. Price £89 (R39) SINGLE POINT. DC MILLIAMMETER $1-0-\frac{\mathrm{fmA}}{}$. Char Fddth 2 Ra. speed: 6 in./ar. Uses typewrer Marker. Main (R52) PEILLITPS 0-10mA 6-CEANNEL DC. Chart width os in (R61/1) TWO PEN. DC MILLIAMMETER. 0-2mA. Chart width (R5) SDNGLE PEN. SERVORTTER MODEL FWS. Chart width 11 in. slow speed. Response (R7) PORTABLE SLNGLE AND FOUR PEN, Suitable recording and 240 in $/ \mathrm{mln}$. : Four pen $1,1,2,4$ and $16 \mathrm{oms} . / \mathrm{aec}$. Electric pens. Mains supply amplifiers to suit.
Price....Bingle pen c/w Amp. E99; Four pen c/w Amp. £149 (R56) SINGLE PEN. DC mulikmmeter. $0-5 \mathrm{~mA}$. Chart widit (R57) SDNaLE PEN. DC MILLIAMMETER. 0 -0.mma. Chart width
8 in . Speed: 1 in. and 6 in ./hr. Terminal Reaistance 4.500 ohma. (58) SINGLE PEN. DC MILLAMMETER, $0-2 \mathrm{~mA}$, Chatit width
 $0-7 \mathrm{~kW}$. Chart width 4 in . Clockwork drive. B-day movement (R34) CAMBRIDGE SINGLE PEN STRIP CHART RECORDER metric recorder for quantikles such an temperature, moisture, ete in. Power supply $200 / 250 \mathrm{~V} 60 \mathrm{~Hz}$. Dimenslons: Wideh 16 ik in , - SNALE Pry Price 26
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(R37) FOSTER STRIP CHART RECORDER TYPE 3480\%. UBe h six-colour half-ineh ribbon and mechanical chopper principle


## METERS

(1517) YTBRON ELECTROMETER. Mod. 33B. Electronic Inst (1614) (I506) AC/DC FOLTMETER. WHSTON ELECTRONTC. Voltag range -7.5 to 10 ...............................rice $\ell 12.10 .0$ (Z508) FLUZ METER Type 15A/AP. TL,G. ELECTRIC. Range
$96-12$ gauge. In wooden case..........................ice elio (I504) VERNLER POTENTIOMETER. TyDe 4363, A. TINSLEY. (1518) WATTMETER. S 67. SANGAMO WESTON, Range $0-15 \mathrm{~W}$
1117) WIDEBAND MLLLVOLTMETER. TF 1871 MARCONL
 (II21) PORTABLE POTENTIOMETER. Type L192828 CAM-
BRIDGE, Fitted with standand cell and themometer. Price f45 (I122) POTENTIOMETER AND GALVO. Type P.3-CROYDON PRECISION. Accuracy .0001
(1123) SLIDE WIRE POTENTIOMETER. CAMBRIDGE. Voltage range $0.01: 0.1=1.0$. Fitted with Galvo. Key. Absolute voltage (132) DECADE INDUCTOMETER. Type 230A. DAWE. Range (II14) MILLIVOLTMETER. Type 264. AIRMEC. Range 0-300 (II11) VALVE VOLTMETER. Type 712. AIRMEC. Range AC
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 (194)
194) DYNOMETER. Type 3206. TINSLEY.......... Price E45 (I95) AC/DC VOLTMETER, Mod, 32. TURNER. Range Voltage
$0-300 \mathrm{~V}, 220 \mathrm{O} / \mathrm{Volt} .5 \mathrm{In}$. moving coll with mirror fcales, in wooden carrying case. . . . . . . . . . . . . . . . . . . . . . . . . . Price $£ 15$
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| Ha2b 1006 | 1300 ohm | 5 amp. | 2 PDT |
| HG2b 1010 | 1300 ohm | 5 amp. | 2 PDT |
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STEP DOWN ISOLATING trana. Standard 240 v AC to 120 v tapped $60-0-6$
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\section*{A. LIMITED QUANTITY OF COMPLETE SYSTEMS AVAILABLE <br> 

SYSTEM SPECIFICATION Scanning standards: 625 line, 50 fields, $2: 1$ interlace. Horizontal resolution: 600 lines. Bandwidth: $8 \mathrm{Mc} / \mathrm{s}$ over complete system. Linearity: $\pm 2 \%$ positional error. Geometry: $\pm 2 \%$ of rectangle averaged over picture. Auto Sensitivity: over the range $60: 1$ in light value-normal picture obtained with illumination of only 2 ft . candles ( $50 \%$ subject reflectance) at lens aperture of $\mathrm{f} / 2$. Spectral Response: Panchromatic. Ambient Temperature: Max. temperature for all units $-30^{\circ} \mathrm{C}$. to $+55^{\circ} \mathrm{C}$. Power requirements $90 / 130 \mathrm{v}$. and $200 / 240 \mathrm{v}$. A.C., $50-60 \mathrm{c} / \mathrm{s}$. Consumption: 45 watts including camera. Camera Lenses: Standard 16 mm . cine lenses with "C" mounts are normally used. Accessories: See under Camera and Control Monitor.


## CAMERA

Totally enclosed dustproof unit only $3 \frac{3}{4} \times 4 \times 10 \frac{1}{2} \mathrm{in}$., weighing 4 lb . Finished in two-tone blue/grey. Vidicon tube. Automatic sensitivity control enables the camera to maintain full picture quality over a brightness range of $60: 1.625$ line scanning standard $2: 1$ interlaced, frame symchronised to mains supply. 600 lines horizontal picture definition with a bandwidth of $8 \mathrm{Mc} / \mathrm{s}$. All supplies are obtained from the control monitor (consumption 5 watts).

## CAMERA ACCESSORIES

Lenses: Superb quality 25 mm . ( 1 in. ) $1 / 1.8$. " C " mount lenses made especially for this system are available, also a limited quantity of motorised 200 m lenses.
Remotely Controlled Weatherproof Pan and Tiht Heads: Pan $340^{\circ}$ at $6^{\circ}$ per sec., Tilt $+50^{\circ}$ at $4^{\circ}$ per sec. $230 / 250 \mathrm{v} ., 50 \mathrm{c} / \mathrm{s}$ operated.
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Weatherproof Camera Housing: Windscreen Wiper, 75 w . heater, internal circulation fan, mounting bracket for camera housing (the latter items are extras for the Weatherproof Housing):

## CONTROL MONITOR

14 in . screen, overall size $16 \times 14 \times 18 \mathrm{in}$. (excluding Remote Control Unit on which Monitor is shown), weight 30 lb . Panel controls provided: Mains on/off, Contrast, Brightness. Remote Focus. Preset controls (under side panels) include: Frequency lock. Monitor height. Frame linearity. Camera height, Camera width. Auto sensitivity, Camera linearity, Cable correction, Video Gain. Beam Current, $Y$ shift, Electrostatic focusing for camera and monitor. Additional input: Video -100 mV peak white positive into 50 ohms: Synch. 2 v . peak/peak negative. Output: 100 mV peak white positive: 2 v. peak/peak- negative. Ambient temperature range $-30^{\circ} \mathrm{C}$. to $+55^{\circ} \mathrm{C}$.

## ACCESSORIES

Remote Control Switching Unit (shown under Control Monitor): Controls auxiliary functions at the camera, i.e. pan/tilt. 200m, windscreen wiper, etc. Size $18 \times 14 \times 3$ in., weight 8 lb .
Distribution Unit: Used for selecting the required picture from those available on the control monitors and distributing it to the appropriate viewing monitor. Size $19 \frac{1}{2} \times 13 \frac{1}{2} \times 8 \frac{3}{4}$ in., weight 30 lb .
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Very powertul ${ }^{7}$ r.p.m.., operates
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Continuously varliabie $30^{\circ}-90^{\circ} \mathrm{C}$, Has senaor burb
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230 VOLT MAINS OPERATED KLAXON HORN This is amsill (about 10in. long) but has a very plercing and
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With these you can vary the voitage applled to your circult from zero to full mains without gencrat ing undre heat. One obviou ex-equipment luol. little used and in every way as good is new. exequipment hul. little used and in every way as gnod ais new.
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Upright mounting, size $3 \times 2 \frac{24}{} \times 2 \mathrm{in}$. approximately. 1.5 gmp . Earth screen between primary and secondaries this transformer will power a 5-5 watt atereo amplifier
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Upright mounting, size approxlmately $2 \frac{7}{6} \times 2 \times 2 \mathrm{in}$, Matching impedance 60 ohms to 15 ohms. 5 watts output
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Primary 500 ohm centre tapped. Ratlo $27 / 1.5$ watts output using twin ELL80 or similar. Price 12/6. No extra for portage if ordered with 56733 .
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76 GnS .
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 Cabinets of latest styling Satin Teak or Atrormosis veneer.
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Ontput rating I.H.F.M. In fully euclosed enamelled case, $\begin{aligned} & \text { approx. } 9 f \\ & \text { facia plate } 10 t \\ & \text { at }\end{aligned} \times 3$ in, and matching knobs. 7 GMS . diagrams and inatructions.
OR FACTORY BULLT with 12 months $\mathrm{g}^{\circ}$ Cee. \&8. 8.19 .9 HIGH QUALITYIR.S.C, COLUN
LOUDS PEAKERS, SPEAKERS In teak or PEAKERS Covered in Rexine and




Attractlve silver finisbed metal lacia plate and matching FULL WIRED
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 Suring Bass, etc. Gram, Radio or Tape. Beserve ITEn, Guitar, for Radio Tuner. Two inputs with associated volume controls so that two separate inpats such as
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Now firmly established as a superb high-fidelity loudspeaker. Design features include the exclusive CELESTION ABR (auxiliary bass radiator), HF1300 treble unit-as used in B.B.C. Monitor Loudspeakers-and specially developed mid/bass unit. Low loss L/C crossover.
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CONDENSERS: $150 \mathrm{mfd}, 300 \mathrm{v}$ A.C., $£ 7 / 10 /-$ each, carr, $15 /-40 \mathrm{mfd}, 440 \mathrm{v}$ A.C. wkg., $£ 5$ each, $10 /-$ post. $30 \mathrm{mfd}, 600 \mathrm{w}$ wg. D.C., $\mathrm{I} 3 / 10 /-$ each, post $10 /-$ $15 \mathrm{mfd}, 330 \mathrm{v} \mathrm{A.C}. \mathrm{wkg.} 15 /$,- each, post $5 /-10 \mathrm{mfd}, 1000 \mathrm{v}, 12 / 6$ each, post $2 / 6$. $10 \mathrm{mfd} 600 \mathrm{v}, 8 / 6$ each, post $5 /-8 \mathrm{mfd}, 1200 \mathrm{v}, 12 / 6$ each, post $3 /-88 \mathrm{mfd}, 600 \mathrm{v}$,
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$\AA 1$ for 5 . Post $2 / 6$. Capacitor: $0.125 \mathrm{mfd}, 27,000 \mathrm{v}$ wkg. $£ 3.15 .0$ each, $10 /-$ post. OSCILLOSCOPE Type 13A, $100 / 250 \mathrm{v}$. A.C. Time base $2 \mathrm{c} / \mathrm{s} .750 \mathrm{Kc} / \mathrm{s}$. Bandwidth up to $5 \mathrm{Mc} / \mathrm{s}$. Calibration markers $100 \mathrm{Kc} / \mathrm{s}$. and $1 \mathrm{Mc} / \mathrm{s}$. Double Beam rube. Reliable general purpose scope, $£ 22 / 10 /$ each, $30 /$ carr.
COSSOR 1035 OSCILLOSCOPE, $£ 30$ each,
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Many types of American Relays available, i.e., Sigma; Allied Controls; Leach;
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TCS MODULATION TRANSFORMERS, 20 watts, pr. 6,000 C.T., sec. 6,000 ohms. Price $25 /-$, post $5 /-\mathrm{d}$
SOLENOID UNIT: 230 v. A.C. input, 2 pole, 15 amp contacts, $\mathrm{f} 2 / 10 /-$ each post 6/-
CONTROL PANEL: 230 v. A.C., 24 v. D.C. @ 2 amps., , $2 / 10 /-$ each, carr. $12 / 6$.
OHMITE VARIABLE RESISTOR: 5 ohms, $5 \frac{1}{2} \mathrm{amps}$; or 2.6 ohms at 4 amps . Price (either type) $£ 2$ each, $4 / 6$ post each.
TX DRIVER UNIT: Freq. $100-156 \mathrm{Mc} / \mathrm{s}$. Valves $3 \times 3$ C $24^{\prime}$ 's complere with filament transformer 230 v. A.C. Mounted in 19in. panel, $24 / 10 /-$ each, $15 /$ - carr.
POWER SUPPLY UNIT PN-12A: 230V a.c. input $50-60 \mathrm{c} / \mathrm{s} .513 \mathrm{~V}$ and 1025 V @ 420 mA output. With 2 smoothing chokes $9 \mathrm{H}, 2$ Capacitors, 10 Mfd 1500 V and 10 Mfd 600 V . Filament Transformer 230 V a.c. input. 4 Rectifying V alves type $5 \mathrm{Z3}$. $2 \times 5 \mathrm{~V}$ windings @ 3 Amps each, and 5 V @ 6 Amp and 4 V @ 0.25 Amp . Mounted


AUTO TRANSFORMER: $230-115 \mathrm{~V}, 50-60 \mathrm{c} / \mathrm{s}, 1000$ watts. mounted in a strong
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POWER UNTT: 110 v. or 230 v . input switched; 28 v . @ 45 amps. D.C. outpur. Wt. approx. 100 lbs, , $£ 17 / 10 /$ each, $30 /$ - carr. SMOOTHING UNITS suitable for above $£ 7 / 10 /-$ each, $15 /-$ carr.
CORPORAL ROCIKET ELECTRONIC GUIDANCE EQUIPMENT: Beacon Radio DRN.7. Rec/Trans. Assembly MX.2048DPW-8. Electronic Control Amplifier AM1510/D] W3. Transmitter C-1493/MRQ.1. Power Units and miscellaneous spares availabic.
MODULATOR UNIT: 50 watt, part of BC-640, complete with $2 \times 811$ valves, microphone and modulator transformers etc. $\$ 7 / 10 /-$ each, $15 /-$ carr.
NIFE BATTERIES: 4 v .160 amps , new, in cases, $£ 20$ each, $£ 110 /$-carr.
FUEL INDICATOR Type 113R: 24 v . complete with 2 magnetic counters $0-9999$, with locking and reset controls mounted in a 3in. diameter case. Price 0-9999, with locking
30/- each, postage 5/-

FREQUENCY METERS: BC-221, meter only $£ 30$ each, BC-221 complete with stabilised power supply £35 each, carr. 15/-. LM13, 125-20,000 Kc/s., $£ 25$ each, carr. 15/-. TS.175/U, £75 each, carr. £1.
CANADIAN HEADSET ASSEMBLY: Moving coil headphones 100 0 , with chamois leather earmuffs. Small hand microphone complete with switch and moving coil insert. New condition. Price 35/- each, post 5/-.
AUDIO OSCILLATOR 382/F: Input 115 v. A.C., $50 \mathrm{c} / \mathrm{s}, 20-200,000 \mathrm{c} / \mathrm{s}$ per sec . in 4 ranges. Cont. wave. Output $0-10 \mathrm{v}$. in 7 ranges. Power output 100 mW . Output impedance $1,000 \Omega$. $£ 27 / 10 /-$ each, $£ 1$ carr.
RACK CABINETS (totally enclosed) for std. 19in. panels. Size: 6 ft . high $x$ 21 in . wide $\times 16 \mathrm{in}$. deep. With rear door. £12 each, £2/10/- carr. OR 4ft. high $\times$ 23 in . wide $\times 19 \mathrm{in}$. deep. With rear door. $£ 8 / 10 /-$ each $_{\text {, }} £ 2$ carr.
CATHODE RAY TUBE UNIT: With 3in. tube, Type 3EG1 (CV1526) colour green, medium persistence complete with nu-metal screen, $£ 3 / 10 /$ each, post $7 / 6$. APNI ALTIMETER TRANS./REC., suitable for conversion $420 \mathrm{Mc} / \mathrm{s}$., complete with all valves 28 v . D.C. 3 relays, 11 valves, price . $£ 3$ each, carr. $10 /-$ ANTENNA WIRE: 100 ft . long. 15/- $+5 /-$ post.
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## DAWE OCTAVE BAND ANALYSER TYPE 1410A

operated. Attenuator 0-50 Db. 6 ranges. $£ 25+£ 1$ carr.
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VRC.19X Trans-ceiver, $150-170 \mathrm{Mc} / \mathrm{s}, 2$ Channel, 20 Watts, Output $12 / 24 \mathrm{~V}$ d.c. operation. General Electric Transmitter, $410-419 \mathrm{Mc} / \mathrm{s}$, thin line tropo scatter system, with antennae. W.S. Type 88, crystal controled, $40-48 \mathrm{Mc} / \mathrm{s}$. W.S. Type
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As a civilian Engineering Assiştant in the Naval Production Pool you'd procure, inspect and test electronic equipment for radio communications, sonar, radar, and missile and weapon control
The job includes preparing production specifications and working closely with contractors to maintain standards: Offices are located in London, Slough and Copenacre, near Bath.
To apply, you should have an ONC or equivalent. The grade you start at depends on the qualifications and experience you have, as there are two levels of entry. Most of the openings, though, are at Grade II. That grade pays $£ 1,643-$ $£ 1,897$. Grade III pays $£ 1,092$ at 21 , rising to a maximum of $£ 1,643$. ( $£ 125$ a year more on all appointments in London.) There is also a non-contributory pension.
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## RADIO OPERATORS

There will be a number of vacancies in the Composite Signals Organisation for experienced Radio Operators in 1971 and in subsequent years.

Specialist training courses lasting approximately nine months, according to the trainee's progress are held at intervals. Applications are now invited for the course starting in January, 1971

During training a salary will be paid on the following scale:

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Free accommodation will be provided at the Training School.
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Excellent conditions and good prospects of promotion. Opportunities for service abroad.

Applicants must normally be under 35 years of age at start of training course and must have a least two vears' operating experience. Preference given to those who also have GCE or PMG qualifications.

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Application forms and further particulars from : Recruitment Officer, Government Communications Headquarters, Oakley, Priors Road, CHELTENHAM, Glos., GL52 5AJ Telephone No. Cheltenham 21491. Ext. 2270

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## TIN

## INDEPENDENT TELEVISION NEWS LIMITEED

## SENIOR ENGINEER-VTR

At the new ITN facilities centre in London. The post is in a small section working with the latest colour equipment and handling the recording, editing and playback of news items received from the U.K. and abroad via Eurovision and Satellite links. The work also involves some colour film recording.
Several years' experience of operation and maintenance of quadruplex VIDEO TAPE RECORDERS is required, preferably under broadcast conditions.

[^12]
## ELECTRONICS SERVICE ENGINEER

is required to service a range of Electronic Desk Calculators at the Sanyo Sales and Service centre in London.
Basic Qualifications: C. \& G. Electronics Service Certificate or equivalent. Consideration would be given, however, to previous experience in this field.
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Write or phone in first instance to: E. J. Landon, Esq.,

Calculator Division Service Manager,
SANYO MARUBENI (U.K.) LTD.,
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## Installation Engineers Technicians \& Testers

Ref. 25720
To test and commission Multiplex, Co-axial Line and Microwave Radio Systems.
Ideal candidates will be less than 45 years of age with practical experience on some of the above equipment. These challenging posts call for drive, initiative and common sense. It is necessary for applicants to be prepared to work anywhere in the U.K.

Applications should be addressed to
The Personnel Officer, STC Chester Hall Lane, Basildon, Essex.

## CONTINUOUS

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## Test Technicians

Ref. 27221
The diversity of products manufactured at the Basildon Plant demands experienced testing staff for work on complex transmission systems.
Candidates should hold an ONC in elec. trical engineering and be able to offer considerable practical experience in the field of testing and fault clearing all types of land-unit, pcm and microwave equipment.

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* Salary £2,010-£2,506 according to experience.
* Low Taxation.
$\star 25 \%$ Gratuity.
* Contract 21-27 months.
* Subsidised accommodation.
* Education Allowances.

The officer will undertake senior operational duties including the maintenance of broadcasting equipment in transmitting stations in remote districts.

Candidates should possess City and Guilds Final Certificate in Telecommunications (with Radio) or equivalent and have wide practical experience of technical broadcasting equipment particularly high power M.F. transmitting equipment.

Apply to CROWN AGENTS; 'M' Division, 4 Millbank, London, S.W.1., for application form and further particulars stating name, age, brief details of qualifications and experience and quoting reference M2K/690995/WF


Men under 35 with experience in light engineering and electronics can build excellent careers in ICL servicing computers.

We want qualified men with HNC or C \& G in electronics engineering, or a Forces training in electronics. Or, perhaps, you have a similar qualification which provesyou have the serious interest in the subject necessary for further specialist training.

We pay realistic salaries while you trainabout six months-on ICL equipment, learning how to sort out operational problems and maintain computers in peak condition.

You will have to take responsibility for highly sophisticated and expensive equipment, so if you have a worthwhile career in mind, here is the chance to apply your expertise and initiative to the full. Career progression and promotion are limited only by your ability.

On top of your basic salary we pay generous overtime and shift rates, plus travelling expenses. Working conditions in ICL are well above the average in industry.

Write giving brief details of your career, quoting reference WW 103 C .
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## If you can put $a^{6}$ Yes' in every box, you might just make a RADIO TECHNICIAN in Air Traffic Control

An all-consuming interest in telecommunications $\square$
At least one year's practical experience in telecommunications, preferably with 'ONC' or 'C and G' technical qualifications


A highly developed sense of responsibility


Willingness to undergo a rigorous programme of training


Aged 19 or over


To the right man, the National Air Traffic Control Service offers the prospect of an interesting and steadily developing career as a Radio Technician in air traffic control.

The work involves the installation and maintenance of some of the very latest electronic equipment at civil airports. radar stations and other specialist establishments all over the country. Important today, the job will become increasingly vital as Britain's air traffic continues to grow. and prospects for promotion are excellent. Starting salary varies from $£ 1.044$ (at 19 ) to $£ 1.373$ (at 25 or over). Scale maximum $£ 1,590$ (higher rates at Heathrow). The annual leave allowance is good, and there is a non-contributory pension for established staff.

If you feel you can.meet the demands of this rather special job-and you have a strong determination to succeed-you are invited to complete the coupon below.

[^13]
## Sea-going Radio Officers can now make sure of a shore job and good pay.



# ASSISTANT ENCINEER GRADEII (BROADCASTING) BOISWANA 

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$\star$ Low taxation
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* Education Allowances

The Posts and Telecommunications Department requires an officer to undertake operational duties including the installation and maintenance of broadcasting equipment in transmitting stations and to assist with the training of junior engineering staff.

Candidates must possess the City and Guilds Intermediate Certificate (Telecommunications) or equivalent and have had five years relevant practical experience, (additional to any period of approved training) of technical broadcasting equipment including M:F. and H.F. transmitting equipment up to 10 KW .

Apply to CROWN AGENTS, 'M' Division, 4 Millbank, London, S.W.1., for application form and further particulars stating name, age, brief details of qualifications and experience and quoting reference number M2K/690420/WF.

## RADIO AND SPACE RESEARCH STATION OPERATIONS SUPERVISOR-

## FALKLAND ISLANDS

An Operations Supervisor is required for service at the European Space Research Organisation Satellite Telemetry Station at Stanley, Falkland Islands. He will be responsible to the Station Director for planning the operation and maintenance of the radio telemetry equipment used for the reception of data from satellites. The grade will be that of Experimental Officer and the post carries a responsibility allowance. The tour of duty will be of three years duration. A hostel is available for single staff and married staff will be accommodated, rent free, in a modern, well furnished, centrally-heated bungalow.
Qualifications Aged 26 or over with a University degree, H.N.C. or equivalent. Experience in the operation and maintenance of electronic equipment and in the management of a small group of staff would be advantageous.
Salary Between $£ 1725$ and $£ 2177$ p.a. To this scale will be added an allowance of $£ 125$, together with a responsibility allowance of $£ 100$ and an overseas allowance.
A car and baggage within certain limits will be transported free of charge.
Apply: The Secretary,
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Slough,
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Telephone: SLOUGH 24411
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This private College provides efficient theoretical and practical training in the above subiects. One-year day courses are available for beginners and shortened courses for men who have had previous training.
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have vacancies in Cardiff for Technical Assistants/ Assistant Engineers in Telecine/VTR and Electronic Maintenance Departments.

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Salary as ACTT. Grade H/E as appropriate.

Apply in writing to:
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Coniract: One year plus leave extensible.
Salary: According to age, experience and qualifications. Commencing at not less than equivalent $£ 2000$ sterling. Free accommodation and passages. Preference for bachelors with tropical experience but not essential.

Interested? Apply for application form to:
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We are growing even bigger in colour television and our factories at Chessington and Bishop Auckland are now producing hundreds of colour sets every week. The next few years will see us growing even more, as colour television spreads throughout the country. Our modern Engineering Department at Chessington, which designs our colour and monochrome receivers as well as all the specialised test equipment, needs two Engineers who are interested in television and wish to join an expanding organisation. The right applicants will have obtained their HNC or equivalent but consideration will be given to day release for those still studying.
Assistance with removal expenses will be given if required.
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Rediffusion Vision Limited
Fullers Way South
Chessington
Surrey

ST. BARTHOLOMEW'S HOSPITAL, LONDON E.C. 1

## Computing Unit for Medical Sciences

## PROGRAMMER

required in the Computing Unit for Medical Sciences which has been set up by St. Batholomew's Hospital and Medical College. The aim of this science-based
Unit is to help enlarge and develop the use of computer technology in medicine, especially in the area of patient monitoring in operating theatres and wards. In this and other applications it is expected that interactive computer graphics will play an important role. The Unit has also an educational commitment. A large-configuration Honeywell ODP-516 is due for installation in the very near future, and will be the latest addition to the computing facilities already available in various departments of both Hospital and College.
Applicants should have programming experience, against a background of electronics, physics or a biological subject. A degree or equivalent qualification is desirable.
Salary scale: $£ 1,100$ to $£ 1,400$ per annum. Applications, accompanied by a full curriculum to the Clerk to the Governors by 3rd September, 1970, quoting reference ASC/2589.

## Electronics Maintenance Engineers

There are excellent opportunities in the Installation and Maintenance Division of U.K. Electronics and Industrial Operations of E.M.I. Ltd., at Hayes, Middlesex, for engineers to carry out maintenance work on a wide variety of electronic equipments including laboratory test gear and trans-ceivers.

Candidates should be between 21 and 45 years of age and have some experience in this type of work. Consideration will be given to experienced Radio and Television servicing technicians and to ex service personnel.

Commencing salaries of up to $£ 1.500$ per annum will be paid and staff conditions include contributory pension scheme and free life assurance.

Please apply in writing giving brief personal and career details to:
J. J. Sweetman, Personnel Department, U.K. Electronics \& Industrial Operations, E.M.I. Ltd., Blyth Road, Hayes, Middlesex.
Tel: 01-573 3888, Ext. 411.

radio..electrical...
electronics engineers

You probably don't realise that your experience and training could put you in line for a key job in the computer world. Right now, you could be a T.V. or telephone maintenance engineer, an ex-
Serviceman with an electronics background or simply have an electrical or electronics qualification providing you have the ability and ambition we'll help you mould your talents into a specialised skill.

Burroughs, one of the largest international electronics companies will train you to become a
member of a highly experienced team of Electronics Field Engineers-men who install and maintain some of today's most advanced computer systems. You can work in your own home area, and at the same time find variety through working with our many clients in the course of your job. And, of course, you will earn a good salary. But, most important of all, you will have true career prospects -because we believe in quickly rewarding talent: .. Promotion to senior management is purely dependent upon ability.

The opportunity is hereif you have the will then we have the way. The rewards are undoubtedly high and we offer a number of excellent employment benefits. including a special company-assisted car purchase scheme. Here are the brief facts-but you can find out more by writing with details of your age. qualifications and experience to: Geoff Lewis,

## Personnel Manager.

 Burroughs Machines Ltd., Dept. WW/S, HeathrowHouse, Cranford Hounslow, Middlesex.
## Glaxo <br> ELECTRONICS TECHNICIAN

Chemical Research

The Physical Chemistry Unit of Glaxo Research Limited requires an electronics technician who will be primarily concerned with the design and building of electronic devices for chemical research. The work will also involve the maintenance and evaluation of modern electronic instruments.

Candidates should preferably possess ' $A$ ' level chemistry and physics and have attained HNC standard in electronics, or be studying for HNC. Further training will be given in the laboratories and day release for further studies is available.
Glaxo offers generous salary scales, holiday and sick pay allowances and welfare and social facilities


Applicants should write giving brief details and quoting reference ZH185 to the Personnel Officer (MRG), Glaxo Laboratories Limited, Greenford, Middlesex.

## ELECTRONIC ENGINEERS

Service Engineers required for Offices, throughout the United Kingdom, of well-known Company manufacturing Electronic Desk Calculating Machines. Applicants should possess a sound knowledge of basic Electronics with experience in Electronics, Radar, Radio and T.V. or similar field. Position is permanent and pensionable. Comprehensive training on full pay will be given to successful applicants. Please send full details of experience to the Service Manager, Sumlock Comptometer Ltd., 102/108 Clerkenwell Road, London, E.C.1.

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## Test <br> Engineers

Due to further expansion we offer excellent opportunities for Test Engineers to make a rewarding career with excellent prospects testing a wide range of complex electronic navigational equipment.
Applicants with a background of T.V. and Radio Servicing, Electronic Control Circuitry and Computers circuits should apply as soon as possible giving details of past experience. An H.N.C. would be an asset
Conditions of service and salaries are excellent

## SENIOR TECHNICIAN (Grade III)

with electrical and preferably some mechanical experience to maintain Therapeutic $X$-Ray equip. ment at the Royal Marsden Hospital, Fulham Road, London, SW3.
The successful candidate will also have the opportunity to develop new equipment.
Minimum qualifications, O.N.C. in Electrical Engineering, and not less than 3 years' technical experience, to obtain salary on scale $\mathbb{E 1 , 2 7 0}$ to £1,590 per annum.
Applications, with details of experience and names of two referees, to the Administrator, the Roya Marsden Hospital, Fulham Road, London, SW3.

## THE UNIVERSITY OF MANCHESTER EXPERIMENTAL OFFICER

Experimental Officer required in the Departmen of Engineering to assist in development and use of high-speed data logging equipment for application to research on internal combustion engines and on fluid mechanics. The equipment will be based upon commercially available units Principal duties are the initial assembly of the equipment, the preparation of control programs, the development of the completed facility, and the supervision of maintenance. Applicants mus have knowledge of and experience in electronic technology. Experience of digital computers and some knowledge of programming desirable, but an applicant judged able to learn could be accepted. Appointment initially for up to three years. Salary $£ 1,370-£ 1,555$ p.a. Further details and forms of application (returnable by August 28th) from the Registrar. The University Manchester, M13 9PL. Quote ref: $166 / 70 / \mathrm{WW}$

## JUNIOR TECHNICAL OFFICER

required for permanent post to assist with commissioning, operation and development of a whole body counter equipped with on line computer processing. Some experience of electronics essential. Age under 30. Two Science ' A' levels, or if over 21 H.N.C. or pass degree. Salary according to age and experience. Write stating full details to Director. Medical Research Council Cyclotron Unit, Hammersmith Hospital, London, W. 12.

## TECHNICAL ASSISTANT

A vacancy occurs in the Medical Electronics Department, St. Thomas Hospital, for a technical assistant, aged 18 to 26 .
The work is concerned with the construction and testing of experimental electronics equipment. Some workshop experience is necessary, and wiring/ assembly experience would be an advantage. Salary on scale $£ 683-£ 1,454$ plus £ 125 London Weighting. This is a Medical School appointment but applicants should write in the first instance to the Personnel Officer, St. Thomas Hospital, London, S.E.1. quoting ref. L/28.

698

UNIVERSITY OF BRADFORD AUDIO VISUAL AIDS UNIT Applications are invited for TELEVISION ENGINEER
(Ref: $A V A / E / / Z$ )
to be responsible for all aspects of the operation and maintenance of closed circuit television equipment includ ing studio practice. The person appointed will possess of relevision, including cameras and videorecorders. He will probably be a graduate or possess an appropriate or I.E.R.E.
Five-day week. Salary on scale rising to $\mathbf{Q 2 , 4 2 7}$ dependent upon qualifications and experience.
Further particulars and application forms returned as soon as possible) from the Personnel Officer. University of Bradford, Bradford, Yorkshire
BO7 IDP.

## BBC

have a vacancy for an

## ENGINEER

## in the Designs Department

Candidates for this post will be engaged in the design of new systems, equipment and test apparatus for use at radio frequencies including both television and audio applications.

Applicants must possess a University degree or equivalent qualification. Experience of transmitter and receiver techniques is desirable, together with a good knowledge of circuit theory.

Salary, depending upon experience, would be initially between $£ 2,395$ and $£ 2,625$ p.a. rising to a maximum of $£ 2,970$ p.a. Candidates with limited experience will also be considered but may be appointed on a salary scale from initially $£ 2,150$ to $£ 2,346$ p.a. rising to a maximum of £2,640 р.а.

Applicants should be citizens of, and permanently resident in, the United Kingdom.

Requests for application form to The Engineering Recruitment Officer, BBC, Broadcasting House, London W1A 1AA
quoting reference YO.E. 22 53. W.W.

# Microwave Installation Controller 

This high-level appointment carries responsibility for planning and controlling the installation and commissioning of 7 GHZ and 11 GHZ systems. ITA, the BBC, the Post Office and HM Government are among the organisations purchasing this equipment.

Resulting from expanded operations in this sphere, the position demands a professional approach based on several years experience in the broad-band field-and proven success in major microwave projects.
Salary will amply reflect the considerable degree of responsibility involved. Excellent fringe benefits are another attraction-but perhaps the most important factor is that present large-scale Pye Telecom growth is creating tremendous opportunities.
Pye Telecom is an ideal Company for ambitious people. If your background suits you for this job, write now, giving career and present salary details, to: M. W. Timmins Esq.,

## UNIVERSITY RESEARCH ASSISTANT

Post for Electronic Engineer available for development and maintenance of electron micro-analyser and other specialised equipment. Thorough knowledge of both linear and digital transistor or circuitry essential. H.N.C. standard or equivalent experience required. Full details from:

## Dr. E. T. HALL

Research Laboratory for Archaeology 6 Keble Road, Oxford Interviews starting 14.9.70

## SOUTHAMPTON GROUP HOSPITAL MANAGEMENT COMMITTEE AND

BOURNEMOUTH AND EAST DORSET
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## TECHNICIANS AND ENGINEERS FOR ST. ALBANS AND LUTON QUALIFIED OR NOT!

VACANCIES exist for work on testing and calibrating valve and solid-state electronic measuring equipments embracing all frequencies up to u.h.f. in Production, Service and Calibration departments
APPLICATIONS are invited from people of all ages with experience or formal training in electronics and from ex-Armed Services technicians.
HIGHLY COMPETITIVE SALARIES, negotiable and backed by valuable fringe benefits.
RE-LOCATION EXPENSES available in many instances.
CONDITIONS excellent; free life assurance, pension
Applicants should be sultably qualified for the following posts in the Electronics Department at Southampton schemes, canteen, social club. $37 \frac{1}{2}$-hour, 5 -day, office-hours week.
(i) ELECTRONICS TECHNICIAN I (qualifications: H.N.C., City and Guilds Final or equivalent qualification);
(ii) ELECTRONICS TECHNICIAN IV (qualifications: .N.C. or H.N.C. or membership of the Society of Radiographers);
(iii) STUDENT TECHNICIAN

Salary Scales: (i) $\mathrm{El}, 800$ by five annual increments to
(ii) 61,020 by eight annual increments to (i) E1,310;
(iii) Salary applicable to age

This department is concerned with the installation testing and maintenance of an extensive range of diagnosefecherapeutic and allied electronic equipment and ultimately with research and development of bio-medic Applleations giving full details-including qualification experience and names of two referees-to the Group Engineer, Southampton Group H.M.C. Coxford Road, Southampton, SO1 6.JW, by the 21 st August 1970.

WRITE or phone Personnel Department stating age, details of previous employment, training, qualifications, approximate salary required, quoting WW 6


## 星 <br> A real opportunity for all Service and Calibration Engineers

Are you capable of working on sophisticated electronic telecommunications equipment?-If you are read on, as Our Technical Service Department has vacancies for Service and Calibration Engineers with at least 3 years experience in the Industrial repair and calibration fields.
Ideally the right men will possess either H.N.C., C. \& G. Full Tech., O.N.C. or equivalents. Salaries will be related to experience and qualifications whilst excellent prospects for promotion exist for the right man. Informal discussion will be held at our main offices, write giving full details to:

> Manager,
> Technical Services Department,
> Aveley Electric Ltd.,
> Arisdale Avenue,
> South Ockendon, Essex.

每Experienced engineers in Design and Development, Systems Test. Technical Sales, Production Engineering, Field Service or Technical Writing should Contact Electronics Appointments Ltd. and we will help you. Our placement service is professional, specialised and completely confidential. We are in consultation with over 800 companies on all aspects of electronics engineering. Phone or write at any time quoting WW 101.
NORMAN HOUSE - 105/109 STRAND • LONDON • W.C. 2 TEL: 01-836 5557

## REDIFFUSION

## COLOUR TELEVISION FAULTFINDERS \& TESTERS

We have a number of vacancies in our Production Test Departments for experienced faultfinders and testers.
Knowledge of transistor circuitry and experience with Colour Receivers together with R.T.E.B. Final Certificate or equivalent qualifications required.
These will be staff appointments with all the expected benefits.
Applications to:
Works Manager, Rediffusion Vision Service Ltd., Fullers Way South, Chessington, Surrey (near Ace of Spades).

## MEDICAL ENGINEERING IN HOSPITALS

## MED BAL ELEMTQNAG

 TECHNICIAN required in the Northampton Group of Hospitalsto service, repair and calibrate a wide range of electronic equipment used in hospitals for medical, surgical and engineering purposes.
Candidates should have good practica experience in radio/telecommunications, pulse generation, automatic control systems or electro-medica equipment. Possession of HNC or HND in electronics or a comparable qualification would be an advantage. Opportunities for further study and training available. Salary scale $£ 1,180$ £1,500.
If you are interested in receiving further details of this opportunity, please write to the Group Secretary, Northampton and District Hospital Management Committee, General Hospital, North ampton, NN1 5BD.

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## UNIVERSITY OF DURHAM <br> DEPARTMENT OF APPLIED PHYSICS AND ELECTRONICS

## EXPERIMENTAL OFFICER

Applications are invited for the post of EXPERIMENTAL OFFICER in ELECTRONICS from Oetober, 1970, Applicants should be experienced conductor Devices. The person appointed will assist in the design and development of electronic circuits for applications in the Department, and will be given an opportunity to take part in teaching.
 EI,S05 per annum with F.S.S.U.
Applications ( 3 copies), together with the names and addresses of three referees, should be sent by Friday, 28 August, 1970, to the Registrar \& Secretary, Old Shire Hall, Durham, from whom further particulars may be obtained.

745


#### Abstract

SITUATIONS VACANT A FULL-TIME technical experienced salesman reA quired for retail sales; write giving detalls of age, Henry's Radio. Ltd., 303 Edgware Rd.. London. W. 2 .


A PPLICATIONS are invited for the post of Technician A In the Department of Psychology. The vacancy is for either a Workshop Techniclan with experlence in metal working and general workshop techniques or an
animal technician. The salary will be on the scale animal technician. The salary will be on the. scale depend on qualifications and experience. Apply in writing, quoting T.25, to Assistant Bursar (Personnel), University of Reading. Whitenights, Reading RG6 2AH,

A RE YOU INTERESTED IN HI FI? If so, and you Trade, an excellent onportunity awaits you at Telesonic Ltd., 92 Tottenham Court Road, London, W.1. Tel. $01-387$ 7467/8.
A SENIOR Transformer/Rectifler design Engineer is A required for varied and interesting projects associated with equipment up to $150 / k V A / K W$. We are an
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REDIFON LTD, require fully experienced TELER COMMUNICATIONS TEST ENGINEERS and ELECTRONICS INSPECTORS. Good commencing salarles. We would particularly welcome enquiries from ex-Service personael or personnel about to leave
the Services. Please write giving full details toThe Personnel Manager, Redifon Ltd., Broomhill Road, Wandsworth, S.W.18.

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UNIVERSITY OF OXFORD, Department of Nuclear to Physics, has a vacancy for a Senlor Technician to join a group designing, builing and maintaining by researchers in nuclear structure employing a twenty million volt accelelerator. Experience in electronics is essential: and a formal quallification an advantage. Salary on a scale rising to 21,592 with six weeks' pald leave per year. Write to T. L. Green, Nuclear Physics Laboratory, Keble Road, Oxford. Mentioning reference A. 133

UNIVERSITY OF LONDON KING'S COLLEGE, TECHNICAL ASSISTANT Required Reecording Unit. Recording Unit and for the organisation and maintenance of audio-visual alds within the Faculty. Applicants should have had experience in the maintenance of electronic equipment. The salary will be in accordance with the scales of College technicians and will be within the range $\boldsymbol{£ 1 , 2 3 5 - \boldsymbol { £ } 1 , 4 0 3 \text { per annum, including }}$ London Weighting. The appointment will be for one yearticulars from the Head Clerk, King's College London, Strand, WC2R 2LS. Closing date for applications: 21st August, 1970 . [726 JNIVERSITY OF SURREY. DEPARTMENT OF TECHNICIAN the Electronic and Electrical Engineering Department to service a wide range of electronic equipment and to build specialised electronic research apparatus. Applicants for the senior position should have had sufficient work with the minimum of supervision. Appolntments will be made on one of the following salary scales: Technician: £935-£1,303 per annum. Senior Technician: $£ 1,278-$ \& 1,586 per annum. Applications in writing should be sent to the Staff Officer, University of Surrey, Gulldford, Surrey, from whom application
forms may be obtalned.

SIGNALS OFFICER, MALAYSIAN GOVERNMENT, whose post is being Malaysianized, seeks employment from the end of the year. Five years head of signals and administrative personnel enzaged in operating and maintaining large rural HF/VBF communications network. Sound experience in the design, equlpping and operation of a system comprising Colitns, Racal, Redifon and Marconi equipment. This experience includes the preparation and general supervision of maintenance programmes and training of junior staff. Administrafor control of staff, budget, estimates. administration and technical detalls of Department communications, Knowledge of government bureaucracy and versed in the writing of reports. Able to conduct offial correspondence in nearly fluent Malay. Age 28 and single. Presently resident Malaysia. Seeking employment in opportunities for promotion of more consideration than salary. Reply to Box WW 740, Wireless World.

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BUILD IT in a DEWBOX quality plastics cabinet. $02 \mathrm{in} . \times 21 \mathrm{in}$. $X$ any length. D.E.W. Ltd. (W), Wingwood RC. FERND
COLOUR T.V. large-screen projectors, Cintel Model 20630. 6 it . picture from R.G.B. Video inputs. DisPhone 01-948 1414. Cor sale. Panels, Units, Components, Meters, Lists. Mr. Frear, 1 Newton Street, Ulverston, Lanc

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Murphy TR 1005,35 Murphy 960,12 Murphy 821,2 Murphy TR 1005,35 Murphy 960 , 12 Murphy 821 , 2 made to The Purchasing Officer, The East Midlands Electricity Board, 398 Coppice Road, Arnold, Nottingham NG5 7HX, from whom further details may be obtained.
Musicar, MIRACLES. Send S.A.E. for detalls of M1 Cymbals and Drum Modules, versatile independent bass pedal unit for organs, pianos or solo, musical nents list reed switches etc. D.E.W. Lid., 254 Ringwood Road, Ferndown, Dorset. [95 NEW CATALOGUE No. 18, containing credit vouchers surplus electric and mechanical components, price $4 / 6$, post free. Arthur Sallis Radio Control Ltd., 28 Gardner Street, Brighton, Sussex.
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STC Star Radiotelephone, single channel UHF, com716 Wireless World.
SET of 3 ( 2 In operating condition) "Fleming" Bright Wireless World.
TV Tubes and parts: $14^{\prime \prime}, 17^{\prime \prime}$ and $21^{\prime \prime}$ Tubes 45/-, LOPTS, scan coils tubes 65/- tested and guaranteed. $19^{\prime \prime}$ and $23^{\prime \prime} 50 /-$ Many obsolete makes in stock. C.W.O, add $10 /-\mathrm{p}$, and p . for tubes, $5 /-p_{\text {. }}$ and $p$. other parts. Personal callers welcomed. VISION CTTY, 146a Goldhawk Road, Shepherds Bush, London, W.12.
Telephone: 01-743 8388.

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Our test department is expanding. It is responsible for the testing of magnetic storage devices, high-speed printers, punched-card and paper-tape equipment

For people with experience in electronics, opportunities exist immediately. Further vacancies will arise over the next few months. Training will be given to those who do not have previous computer experience

Applicants must have worked on the testing, maintenance or repair of electronic equipment, and preference will be given to those qualified to ONC. (Elect.) or C \& G Final.

Locations: Kidsgrove and Winsford. Both are situated in rural surroundings bordering on the Cheshire Plain. Housing is available at attractive prices, and assistance with mortgage can be arranged.

Write giving details of age, qualifications, and experience, to: Brian Buckley, Personnel Manager, International Computers Limited, Kidsgrove, Stoke-on-Trent, quoting reference WW 498M

## TECHNICIAN <br> MICROWAVE/RADIO TELEMETRY SYSTEMS

## The West Midlands Gas Board uses microwave radio

 equipment, digital supervisory systems and U.H.F. radio scanning gear for telemetry and data transmission throughout the West Midlands area. V.H.F./U.H.F. mobile $R / T$ systems are operated from fixed and mobile transmission centres and are extensively utilized by the service and conversion departments.We require a Technician grade 1 to assist in the maintenance and commissioning of our equipment. Knowledge of comprehensive modern testing procedures, appropriate maintenance experience and the ability to work alone to effect site repairs are essential. A current driving licence is required.

Initial salary £1,365-£1,725 p.a. with excellent conditions of employment including progression to Senior Technician and up to $£ 1,968$ p.a. on proven ability.

Please apply quoting ref. WW/A90 to the Senior Personnel Officer (Headquarters), West Midlands Gas Board, 5 Wharf Lane, Solihull, Warwickshire.

## TELECOMMUNICATIONS ENGINEER

A Telecommunications Engineer is required by a company manufacturing H.F. antennas. It is anticipated that the successful applicant has C. \& F. full certificate, H.N.C. or degree, and preferably has.some installation or similar experience in telecommunications.
The applicant will be expected, after training, to be able to prepare quotations, customer liaison, design minor modfications, supervise our workshop, liaise with suppliers and occasional supervision of installations.
The anticipated age range is 25 to 35 . Salary negotiable. For proven results generous annual bonus on profits will be given and also the opportunity of becoming a Director of the company.
Contact the Managing Director.

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## ELECTRONICS TECHNICIANS

## Department of Phystes

Senior Technician required to join a small team carrying out research into the applications of nuclear science, concerned with a wide variety of electronic counting and measuring equipment. Candidates should possess good experience and preferably qualifications in the design, construction and maintenance of modern electronics. Some experience of computer interfacing an advantage. Ref.: I I 3/B/447. Senior Technician/Technician required for the construction and maintenance of advanced electrical equipment. Qualifications and/or experience in pulsed digital equipment desirable. Ref.: $113 / B / 448$ Salary ranges
Senior Technician .. $£ 1,278$ to $£ 1,586$
Technician ... $£ 935$ to $£ 1,303$ Apply: Assistant Secretary (Personnel), Personnel Office, University of Birmingham, P.O. Box 363, Birmingham, BI 52 TT.

## TECHNICIANS

The Margaret McMillan College of Education requires the following:
AUDIO VISUAL AIDS TECHNICIAN-GRADE 2 -to be responsible for the maintenance and repair of audio visual aids equipment.
Candidates should preferably possess City and Guilds Radio and Television Servicing Intermediate Certificate.
JUNIOR TECHNICIAN-GRADE 1-to assist in the maintenance of equipment and making of teaching aids. An interest in craft, e.g. woodwork, would be an adrantage and candidates should preforably have 3 G.C.E. ('O' level) passes in appropriate subjects.
Salaries are in accordance with the N.J.C. Technicians' Grades, namely:

Grade 2- 5942 to 11,089
Plus a qualification allowance of either $£ 30$ or $£ 50$ per annum where appropriate.
Application forms and further details of the posts may be obtained from the. Senior Administrative Officer, Margaret McMillan College of Education, Trinity Road, Bradford 5, and should be returned within 14 days of the appearance of the advertise-
ment.

UHF, COLOUR and TV SERVICE SPARES. Leading British makers' surplus Colour Frame and Line time base unlts Incl. EHT transformer, £5, carriage tuner, 4 transistors, knobs, circuit data. Easily adjusted for use as 6 position UHF tuner, $£ 4 / 10 /-$, $P / P 4 / 6$ MURPEY $600 / 700$ series complete UEF conversion kits nacl. tuner, drive assy, 625 IF amplifier, 7 valves, accessories. housed tn speclal cabinet plinth assembly £ $7 / 10 /-$ or less tuner $£ 2 / 18 / 6$, P/P $10 /-$. SOBELL/GEC 405/625 switchable IF amplifier and output chassis, $25 /-$, P/P $4 / 6$. Phillips 625 IF AMP panel and circult 25/- P/P 4/6. Philips 625 IF AMP panel and circuit drive assy, aerial panel, $\dot{\&} 5 / 10 /-, P / P 4 / 6$. New op manufacturer tested VAF tuners, AT7639 Peto Scott Decca, Ekco, Ferrant1, Cossor, 38/6, Cyldon C 20/-, AB miniature with UHF injection 25/- Ekco 283/330, Ferrant1 1001/6 25/-. New freball tuners, Ferguson HMV, Marcond type 37/6, Plessey 4 position push button tuners with Ukir injection, incl. valves, 58/6. Man channel coils. Surplus Pye, Oltra, Murphy, $110^{\circ}$ scan colls $30 /-$. Sobell $110^{\circ}$ Frame $O / \mathcal{P}$ transformers $17 / 6$, $\mathrm{P} / \mathrm{P}$ 4/6. Transistorlsed time base panel for Ferguson portable $50 /-, P / P$ 4/6. LOPTs, Scan Colls, FOPTs available for most popular makes. PYE/LABGEAR
transistorised booster units $\mathrm{B} 1 / \mathrm{B} 3$ or UHF battery transistorised booster units B1/B3 or UHF, battery despatch available. MANOR SUPPLIES, 172 WEST END LANE, LONDON, N.W. 6 (No. 28 Bus or W. Hamp stead Tube Station), MAIL ORDER; 64 GOLDERS AANOR DRIVE, LONDON, N.W.11. Tel. 01-794 8751 Staff holidays August 17 to 31 .

UNMARKED Silicon N.P.N. Transistors $60 \%$ guaran teed O.K., 50 for 10/-, P.P. 1/6. Electrolytic capact tors $100+250+10 \mu \mathrm{~F}, 250$ volts, $4^{\prime \prime} \times 13^{\prime \prime}, 8 / 6$, P.P. $1 / 6$ Free bargain lists ready early September. Shop closed rom 27 th August to 2nd September. Elekon Enterprises 29 Tottenham Street, London, W1P 9PQ. Tel 01-580 7391.
$60 \mathrm{kc} / \mathrm{s}$ Rugby \& $75 \mathrm{kc} / \mathrm{s}$ HBG Neuchatel Radio Re units, $£ 35$. Tcolex, 6 Warwick Close, Hertford (4856)

## CAPACITOR DISCHARGE IGNITION

(W.W. JAN.)

Invertor transformer 30VA 15:1 ratio. CWO 32/- + 5/- p.\&p. Also available with $30: 1$ ratio for 6 V systems, cost as above. MAGTOR LTD., 68 Dale Street, MANCHESTER

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FOUNG ELECTRONIC ENGINEER, resident Kingston-upon-Thames area, owns tools and instruments,
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## TEST EQUIPMENT - SURPLUS ANDSECONDHAND

DAWE TYPE 1400 E sound level meter, almost new, 10 with hide case and manual. \& 60 . Phone 769-2658 SIGNAL generators, osclloscopes, output meters, wave Noltmeters, frequency meters, multi-range meters, etc., etc., in stock.-R. T. \& I. Electronles, Ltd., Ash-

## RECEIVERS AND AMPLIFIERS-

SURPLUS AND SECONDHAND
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[^15]
[^0]:    * Philips Records Ltd.

[^1]:    * From Latin trans (across), ducere (to draw).

[^2]:    + From Latin digitus (finger). The link with counting is obvious.
    $\neq$ From Greek ana (up to), logos (proportion).

[^3]:    * With one exception; see this page, May issue.
    $\dagger$ ("Management and Merger Activity" by Gerald Newbould.)

[^4]:    "See "B.B.C. Band-two Broadcasting Stations", in the August issue, page 401.

[^5]:    $\dagger$ For further reading: "F-M Simplified" by Milton S. Kiver. Published by D Van Nostrand Co. Inc. Princeton, New Jersey, U.S.A.

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