PRACTICAL
FEBRUAFY 19E5 - P1-00


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SPAGTRUM
DAG/ADC BOARD
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cENERATOR
F-V CONV =RTER
MICROWRITNG
The Principle and the Product

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## THIS MONTH'S COVER...

Our cover photograph shows silicon wafers in a furnace during the production of integrated circuits. Photograph courtesy of National Semiconductor.


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For contralling motorised garage doors and switching
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Lots of appli
cations like
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and TVs
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normally open relay output plus iwo latched transistor outputs. battery powered transmitter a
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| PN8 | Tone $\&$ Volume Control | ¢13.60 |
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## INFRA.RED REMOTE CONTROL KITS



These kits are designed to enable infra red remote control to be incoiporated into virtually any application from switching car locks or alarms to controlling Hi.Fi or TV. The application will determine the interface cricuitry between the recerver and the controlled device. General in structions and applications are supplied The kits are coded and provide a high dearee of security and noise immunity MK 11 MK 12 receivers. Requises PP 3 bat MKy Size $8 \times 2 \times 13 \mathrm{cms}$ Range approx 60 ft . C . 8.80 Keyboards for MK 18
MK 94 -way for use with MK 12 £ 1.90 MK 10 16. way for use with MK 12 E5. 40 MK 13 11-way for use with MK $11 \quad € 4.35$ MK11 Receiver Kit mans powered Provides 10 taiched plus 3 analogue out puts ideal for controlling audio amplitiers. TV or lighuing where control of light
brightness is required
$£ 13.50$ brightness is required
MK14 AC Power Controller Kit (phase) controlling AC loads from MK analogue outputs. eg lamp dimming

\section*{COMPONENT.PACKS PACK 1650 Resistors 47 R 10M PACK 240 per value

10.1000 V Elecr:al 5 per <br> 10. 1000 HF 5 per <br> PACK 360 value Polvester Capa <br> citors 001 luF 250 V <br> 5 values <br>  <br> $\Rightarrow$ <br> - $x$}

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111.50

Electric Lock Mechanism for use with existing door locks and the above kit. Requires relay 112 V AC/DC coil (701 150)
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HOME LIGHTING KITS

These kits are
designed to
eplace a stan ard wall switch 300 w of lighting

TDR300K Remote Controllede Light Dimnier
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T0300K Touch Dimmer $£ 7.75$
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D300K Rotary controlled
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c3.95

## DISCO LIGHTING KITS

DL 1000K - This value-for-money 4 -way chaser features bi directional sequence
and dimming. 1 kW per channel. $£ 15.95$ and dimming. 1 kW per channel. $£ 15.95$
0 L 21000 K - A lower cost uni-directional verslon of the above Zero switching to reduce interference Optional opto input altowing audio beat OC Volts: 0-0.2.2-20.200.1000 AC Current: 0.200 mA .0 .10 A . DC Curtent: $0-200 \mathrm{~mA} / 0-10 \mathrm{~A}$. R . M Size: $160 \times 85 \times 29 \mathrm{~mm}$
(405 206)
High Sensitivity Temperature Probe For use with a multimeter to measure temperatures from $-50^{\circ} \mathrm{C}$ to $+250^{\circ} \mathrm{C}$. Accuracy: $1.5^{\circ} \mathrm{C} @ 25^{\circ} \mathrm{C} .2^{\circ} \mathrm{C} @ 100^{\circ} \mathrm{C}$ fesponse time (in wateri. 5 seconds. Includes case, calibrated scale and in-
ight response (DLA/1)
DL3000K -3 - channel sound to light kit features zero voltage switching, auto phone. 1 kW perchannel $\mathbf{£ 1 2 . 9 5}$

DVMIULTRA SENSITIVE THERMOMETER KIT
AC Volts: 02.20 ing case supplied
[44.85
Auto Ranging. digit 10 mm display Continuity buzzer. and range indication. 10A internal shunt for ACIDC current measurement. Carry

Based on the ICL 7126 and a $31 / 2$ digit hiquid crystal display, this kit will form the basis of a digital multimeter lonly a few additional resistors and switches are required - details supplied), or a sensitive digital thermometer $150^{\circ} \mathrm{C}$ 10 $+150^{\circ} \mathrm{C}$ )

reading $0.1^{\circ} \mathrm{C}$. The kit has a sensitivity of 200 mV for a full-scale leading automatic polarity and overload indication. Typical | polarity and overioad indication. Typical |
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| battery life of 2 years (PP3). |
| 15.50 |

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## SAFETY

E
LECTRONICS has done much to - benefit our way of life and standard of living in all areas from entertainment to safety at sea and in the air. Of course it has also enabled development of more sophisticated weapons and defence systems but that is another story. Our exploration of space is totally dependent on electronics and navigation about our own planet is also now based mainly on high technology.

What a pity then that the modes of transport we all use every day have not benefited more from the introduction of electronics to aid safety. The car you drive may have a computer to show fuel consumption, it may have a talking dash panel or even an engine management computer, but have the electronics been used to improve safety? How many vehicles are fitted with an anti-locking braking system? How often do you see vehicles skidding even on dry roads? How often do the back wheels of unladen lorries lock up when they stop? How many motorcyclists come off in the wet when braking or skid into the back of the car in front?

Admittedly many of the skids that do occur result in no damage or injury but of course some do. Surely it is better to make vehicles safer with an electronically controlled failsafe braking system than to get them talking to you? This is one area where the amateur in electronics can do little himself. We would not encourage readers to modify any
vehicle braking system, so we cannot fit a system to help ourselves.

The sad thing is that the technology and mechanics to perform the necessary tasks has been around for some years. Perhaps the manufacturers feel we will not pay for the extra safety; maybe they do not feel it is necessary? The next time you see a minor skid that could have been dangerous, a motorcyclist fall off, or a lorry stopping slightly sideways just think about what could have gone badly wrong and see if you feel anti-skid braking would be worth another couple of hundred pounds on the already inflated price of a new vehicle in the UK.

## LEGISLATION

Maybe you will even think that legislation would be a good thing, even if it might not save as many lives as compulsory seat belt wearing!

Incidentally, the motorcyclist I saw come off this morning was shaken but not badly injured, although his bike was probably a write-off and the car he ran into badly damaged. Think about it if you buy a new vehicle! The extra cost could be worth the time, trouble and heartache alone.


## BACK NUMBERS and BINDERS...

Copies of most of our recent issues are available from: Post Sales Department (Practical Electronics), IPC Magazines Lid., Lavington House; 25 Lavington Street, London SE1 OPF, at $£ 1$ each including Inland/Overseas p\&p. Please state month and year of issue required.

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Components are usually available from advertisers; where we anticipate difficulties a source will be suggested.

## Old Projects

We advise readers to check that all parts are still available before commencing any project in a back-dated issue, as we cannot guarantee the indefinite availability of components used.

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We regret that lengthy technical enquiries cannot be answered over the telephone. unless otherwise specified. Prices correct at time of going to press.

## HIGH CGST IMSULITION

Most constructors will be painfully aware of the annoying shrink-back properties of insulation, encountered when soldering wires into place. Over the years manufacturers have developed heat-proof insulation materials for specialised cable applications which eventually filter through industry to the home-constructor-and very welcome they are, too. It.may surprise you to know, however, just how far, and to what expense, manufacturers will go in order to optimise the insulating properties of the materials they use.
B.I.C.C. for instance has just completed the installation of a new electron beam accelerator plant at its Electronic Cables factory in Cheshire, the cost? A staggering £2. 5 million. The facility is considered to be the most sophisticated and versatile of its kind in the Western world. The accelerator produces high velocity electrons which have sufficient energy to penetrate the cable insulation.

Once inside a polymeric insulation, the electrons initiate chemical reactions which lead to the formation of chemical bonds or crosslinks. Increasing the number of crosslinks leads to eventual formation of a three-dimensional network which substantially enhances the physical properties of the insulant.

The most obvious effect of crosslinking is that the material loses its thermoplastic characteristics and becomes a non-melting

thermoset with a better balance of mechanical properties at both high and low temperatures; chemical resistance is also enhanced.

The whole facility is enclosed in 1500 tonnes of concrete for personnel protection during plant operation. The picture shows the plants computer control room.

# TKTEIEVISOON MONTIOR 

The latest in the TX range from Ferguson is a 14 inch monitor/colour television. It will offer those who can afford a second or even third set a very flexible visual display tool.

The MCO1 has separate RGB, composite video and aerial inputs enabling the user to get the best possible display from broadcast TV, video recorders, teletext and home computers.


Perhaps the most interesting of these options is the ability to directly connect a home computer without the modulation/demodulation problems that occur when using a standard TV set. It must be borne in mind that not all currently available home computers have a direct video output. The machines without this facility have on-board modulation/demodulation and were so designed for use with a visual display medium that most people already possessed-a standard TV set.

The provision of separate RGB, composite video and aerial sockets also allows the home computer, video recorder or game and TV aerial to be connected simultaneously; the set senses the signal selected and switches to it automatically.

A range of special connector leads is available to cover the different home computer options. The set is manufactured in the UK at the company's Gosport plant. It is expected to retail at circa $£ 230$.


All too often the most worrying aspect for the creator of an original design is, how to protect that idea from those who would copy and exploit it for their own gain. This has been the case since the first inventor brought forth a brainchild, only to stand by helplessly as someone else marketed his idea and made a fortune. The laws governing Patents, Trademarks, Designs and Copyright are complex indeed, without guidance the layman may be forgiven for getting confused. Laurence Shaw's recently reprinted guide can be of great help to inventors and innovators alike.

The Practical Guide for people with a new idea is a book which explains in clear language how to protect a new idea, product or scheme and exploit it to the full. Market research, approaching a manufacturer, telling the world about an idea without losing your rights and patenting an invention are all covered together with secret patents.

This publication is available from booksellers at $£ 5.50$, or by mail order at $£ 5.95$ from The Patent Eye, George House, George Road, Edgbaston, Birmingham B15 1PG. (021 454 2165).

## MAGIC LANTERN

Question: If you are exposed to radiation do you glow in the dark? Answer: Of course not. Not unless you are first coated with a phosphor of some kind. It is a useful fact that beta particles from a radioactive source will, when they strike a phosphor such as zinc sulphide, cause light to be emitted from it. Battelle's Pacific Northwest Laboratories are lesting a novel application of this phenomenon. Scientists are evaluating a portable runway lamp for setting up landing strips in out-of-the-way places, or during emergencies in which the electricity supply is lost.

The lamp comprises a glass tube, its inside surface coated with a phosphor, and which is filled with tritium gas, the radioactive isotope of hydrogen. The lamp can not be turned off, it simply continues to glow for the twelve years half-life of the gas. Keeping the glass clean is the only maintenance operation required during that time. The quantity of radioactive material used is so minute that it is harmless even if the glass breaks, it is claimed.

During field tests in Alaska pilots reported that they perceived light from the radioluminescent lamps differently from that of conventional light, and human response now needs to be assessed to find out how useful these lamps may be.

## BTs rumble machine



## It's new from British Telecom, For paging far-off staff. <br> A little pocket thing,

That could well cause a laugh.
You see instead of 'bleeping', It's been made to 'vibrate'.
So you're the only one that knows, HQ and you have got a date.

The waveforms coming through the air, Will go right through your pants.
And trigger-off this rumble-box, Like a herd of elephants.

So if you're in a meeting,
Friends might still get the rise.
When they notice that your eyeballs, Are looking like mince pies.

## HEASSOUWIN

Ensuring peak response and high-quality reproduction, Electrolube's Video Tape Head Cleaner is a safety solvent designed for use on all magnetic tape heads.

The cleaner loosens and removes accumulated deposits of dirt and tape oxide and dries quickly without leaving any residues on the tape. The cleaner is nonflammable, and non-conductive, it will not damage plastics or rubber.

The solvent comes in handy 110 gram aerosols and is conveniently applied by spraying directly onto the heads and mechanisms. In addition, the cleaner is ideal for spraying onto cleaning tapes and other tape cleaning devices, such as cotton buds or felt and chamois leather sticks.

Available on its own at circa $£ 1.20$, or with 25 extra long cotton buds at circa £1.60 from electrical retail outlets.


## BBC's go Bang

Following a tongue-in-cheek comment from Mike Cook, the Technical Editor of Micro User, several hundred BBC micro owners recently returned their machines to their respective dealers, in the fear that they were about to detonate.

The unfortunate comment was printed in the magazine's problem page as part of a reply to a reader's query regarding an 'error message'. Mr Cook, believing himself to be the subject of a "wind-up", answered in kind. "Take your computer immediately to the dealer as this error message indicates that it is about to explode."

The manufacturers, Acorn Computers, were not amused, neither was the middle-aged housewife who reportedly surrounded her machine with a bucket of water.

## POINTS <br> ARISING...

## RING MODULATOR

## December, 1984

Alterations to this project must be made as follows:

In Fig. 9 the component marked C35 should be marked R35.

The capacitor C21 should have its +ve terminal connected to R10.

In Fig. 10 the unmarked component mounted between JK1 and JK2 is R47.

A wire link should be connected between JK3 (C25 -ve) and JK4 (C26 +ve).

Fountidounl...
Please check dates before setting out, as we cannot guarantee the accuracy of the information presented below. Note: some exhibitions may be trade only. If you are organising any electrical/electronics, radio or scientific event, big or small, we shall be glad to include it here. Address details to Mike Abbott.

International Light Show Jan. 14-28. Olympia. E6
British Toy \& Hobby Fair Jan. 18-Feb. 2. Olympia. D6
Component Fair March 10. Carleton Community Cntr., Pontefract (on A1 to Darrington). F2
London Medical March 12-15. Earls Court. S2
IFSSEC (fire/security) April 15-19. Earls Court, London. S
Cast (Cable \& Satellite) April 16-18. NEC, Birmingham F5
Communications April 23-25. Olympia. I
Photoworld April 23-May 6. Earls Court. I
CAD April 26-28. Metropole, Brighton. K2
Fibre Optics \& Lasers April 30-May 2. Olympia. E
Custom Electronics \& Design Techniques April 30-May 2. E

All Electronics Show/ECIF April 30-May 2. Olympia 2. E
Circuit Technology April 30-May 2. E
Field Service \& Repairs April 30-May 2. Olympia 2. E
Automan (manufacturing) May. NEC. T1
Scotelex June 4-6. Royal Highland Soc., ex. Hall, Ingliston,
Edinburgh. A1
Personal Computer World Show Sept. 18-22. Olympia 2. M

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# MODLLAR ADDIO PगH:  

ecent years, improvements in semiconductor technology and, in particular, the introduction of a number of highly versatlle consumer integrated circuits and power Darlington stages', have resulted in audio equipment which is both compact and very straightforward. This new series deals with the construction of a variety of modules for use in the custom design of sound reinforcing systems and for public address work generally.

We start, this month, with full constructional details of a 50 W power amplifier module. This unit forms the basic building block for several complete designs to be described later. Details of suitable pre-amplifiers, line drivers, tone controls and mixers will also be included; the aim being that of affording the individual constructor the widest possible choice of audio system configuration.

## THE 50W POWER AMPLIFIER MODULE

The power amplifier module is electrically robust, is simple to construct, and uses low-cost readily available components. In its basic form, the module is capable of delivering a continuous r.m.s. sine wave output of 50 W into a 4 ohm load. The design may be easily modified for operation with alternative output transistors and/or supply rails, as shown in Table 1.

Whilst every effort has been made to avoid the pitfalls, it should be stated at the outset that this project, together with its higher power derivatives, is not for the faint hearted. Indeed, the prototype amplifier was not developed without a few disasters, including four output transistors which literally melted during the testing stage!

An important requirement of this project (and one which readers ignore at their peril) is that the loudspeaker systems employed should be capable of handling the full amplifier output power. However, readers who do not have immediate access to correctly rated loudspeakers need not despair since we shall, next month, be describing a calibrated test load rated at continuous r.m.s. powers well in excess of 100 W . A dummy load of this type should prove to be an
invaluable accessory for those wishing to "run-up" the amplifier without destroying their ear drums.

Having started on a cautionary note it is perhaps worth saying that, provided readers carefully follow the setting-up procedure and observe the recommendations concerning heat sinks, component ratings, and supply rails, there should be few, if any, problems.

## CIRCUIT DESCRIPTION

A simplified block schematic of the power amplifier module is shown in Fig. 1. The corresponding circuit diagram is shown in Fig. 2. The module consists essentially of a differential input stage followed by a driver and complementary power Darlington output stage. The unit runs from balanced (i.e. separate positive and negative) supply rails with a common OV rail at earth potential.

The input stage is formed by TR1 and TR2 which are connected as a long-tailed differential pair with TR3 acting as a constant current source. The emitter currents of TR1 and TR2 are determined by VR1 which provides a range of adjustment from about 1.5 mA to 3.0 mA total current. The signal input is applied to the base of TR1, via a switched d.c. blocking capacitor arrangement, whilst negative feedback (both d.c. and a.c.) is applied to the base of TR2. The overall voltage gain of the module is determined by the amount of feedback applied and is approximately equal to the ratio of

| Max. <br> r.m.s. <br> output <br> power | Rec. supply rail voltages | Max. rec. heatsink thermal resistance | TR6 (npn) | TR7 (pnp) | T1 sec. rating $2 \times$ |
| :---: | :---: | :---: | :---: | :---: | :---: |
| 30 W | $\pm 30 \mathrm{~V}$ | 4 deg.CM | TIP121 | TIP126 | 20V/1.5A |
| 45 W | $\pm 30 \mathrm{~V}$ | 2 deg.CM | TIP141 | TIP146 | 20V/2A |
| 80W | $\pm 40 \mathrm{~V}$ | 1 deg.C/W | 10 K 80 | 11 K 80 | 25V/2.5A |
|  |  |  | MJ3001 | MJ2501 |  |
|  |  |  | 2N6058 | 2N6051 |  |
| 120W | $\pm 50 \mathrm{~V}$ | 0.5 deg. CN | MJ11016 | MJ11015 | 32V/3A |

Table 1. Output device selection table


# CUSTOM DESIGN YOUR OWN HIGH POWER AUDIO SYSTEM 

## AUDIO PROJECT



R3 to R4
Direct coupling of input signals is provided by means of S1 which bypasses the d.c. blocking capacitor, C1. In order to preserve symmetry of the differential stage, the following resistors are made equal: R2 and R3, R5 and R6, R1 and R4 (note that the latter assumes that the amplifier is fed from a relatively low-impedance source).

TR4 forms a conventional common emitter driver stage using an npn transistor. Since the quiescent power


Fig. 2. Complete circuit diagram of the Power Amplifier Module

## SPECIFICATION

Maximum power output: (measured at 1 kHz )

Minimum recommended load impedance:
Voltage gain:
Voltage gain. for max. rated output:
Input voltage for max. rated output: less than 2 V r.m.s.
Input impedance:
Recommended source impedance: Total harmonic distortion: 50k approx.
600ohm
0.05\% typical at 30W output into 80 hm
Frequency response (a.c. coupled): 15 Hz to 50 kHz at -3 dB
(d.c. coupled): d.c. to 50 kHz at -3 dB less than -85 dB related to max. rated output
dissipation for this stage is in the region of 125 mW , a metal cased TO5 style device is much to be preferred. Bias for the output transistors is provided by TR5 which acts as a constant voltage source, adjustable by means of VR2. The output stage is a conventional complementary symmetricai arrangement using Darlington pairs, TR6 and TR7. A variety of different devices may be employed in the output stage depending upon output power requirements and the available supply voltage rails. These configurations are summarised in Table 1. The output stage is protected by means of two 5A quick-blow fuses, FS2 and FS3. It should perhaps be mentioned that this form of protection is not completely foolproof but will normally cope with a short-circuited load or failure of one of the output Darlingtons.

C6 and R17 form à Zobel network whilst L1 ensures unconditional stability of the amplifier when operating into a severely capacitive load. Bootstrap feedback is applied via C4 in order to raise the effective impedance of the collector load for TR4. C5 provides high-frequency roll-off since the bandwidth of the amplifier is otherwise somewhat excessive. The power supply arrangement is fairly conventional and
provides symmetrical supply rails of nominally +30 V and -30 V .

## CONSTRUCTION

With the exception of the power supply (T1, FS1, REC1, C9 and C10) and the output transistors (TR6 and TR7), all components are mounted on a single-sided p.c.b. measuring approximatly $65 \mathrm{~mm} \times 115 \mathrm{~mm}$. The component overlay of the p.c.b. is shown in Fig. 3. Components should be assembled on the p.c.b. in the following sequence: terminal pins, resistors, capacitors, transistors, pre-set resistors, fuse clips, and inductor. The latter component consists of 20 turns of $20 \mathrm{~s} . \mathrm{w} . \mathrm{g}$. wire wound with an inside diameter of 8 mm . Care should be taken to carefully remove the enamel at each end of this component in order to facilitate an effective soldered connection to the p.c.b.


Fig. 5. Frequency response (8ohm load)

[EE1555P
Fig. 3. Component layout of the p.c.b.


Fig. 4. Wiring diagram for the Power Module

## COMPONENTS

## Resistors

| $R 1, R 4, R 7$ | $4 k 7$ (3 off) |
| :--- | :--- |
| R2,R3 | $47 k$ (2 off) |
| R5,R6 | 470 (2 off) |
| R8 | $10 k$ |
| R9 | 220 |
| $R 10, R 14, R 15, R 16$ | $1 \mathrm{k}(4$ off) |
| R11,R12 | $2 k 7$ (2 off) |
| R13 | 1 k 8 |
| R17 | $100.5 \mathrm{~W} 5 \%$ carbon |

VR1 220 min . hor. skeleton pre-set
VR2 1 k min . hor. skeleton pre-set
Except where otherwise stated, all fixed resistors are 0.25W 5\% carbon.

## Capacitors

| C1 | 220 n 250 V polyester |
| :--- | :--- |
| C2 | $100 \mu 16 \mathrm{~V}$ p.c. electrolytic |
| C3 | $100 \mu 63 \mathrm{~V}$ p.c. electrolytic |
| C4 | $220 \mu 25 \mathrm{~V}$ tubular electrolytic |
| C5 | 33 p ceramic |
| C6 | 100 n 250 V polyester |
| C7.C8 | 100 n 100 V disc ceramic (2 off) |
| C9,C10 | $4700 \mu 63 \mathrm{~V}$ can elect. (2 off) |

## Semiconductors

| D1,D2 | 1N4148 (2 off) |
| :--- | :--- |
| TR1,TR2,TR3 | BC212L (3 off) |
| TR4,TR5 | BC142 (2 off) |
| TR6 | $10 K 80$ (see Table 1) |
| TR7 | 11 K80 (see Table 1) |
| REC1 | KBPC802 (200V/6A) |

## Miscellaneous

p.c.b. s.p.d.t. miniẩture p.c. slide switch

T1 80VA mains transformer with 220 V primary and two secondary windings each rated at $20 \mathrm{~V} / 2 \mathrm{~A}$ minimum (see Table 1)
L1 (see text) p.c. mounting fuse clips (4 off)
FS1 2A 20 mm quick-blow mains fuse and holder
FS2 and FS3 5A 20 mm quick-blow fuses
Heatsinks (see text)
Silicone impregnated heatsink washers \{thermal resist-
tance 0.33 deg.C/W) and bushes (two sets required)
Terminal pins ( 13 required)
SK1 5-pin 270 deg. DIN socket
SK2 and SK3 4 mm sockets (1 red and 1 black)
Mains connector
Printed circuit board (502-01)

The Darlington transistors must be mounted on a substantial heatsink of no more than 1 deg.CW thermal resistance. To facilitate effective heat transfer the use of silicone impregnated washers is highly recommended (it should be noted that the collector connections of the Darlington power transistors are formed by their respective cases and these will have to be insulated from a heatsink which will invariably be at earth potential).

The encapsulated bridge rectifier, REC1, also requires mounting on a heatsink. The requirement for this heatsink is somewhat less stringent than that needed for the output transistors and a rating of 5 deg.C/W (or approx. $110 \mathrm{~mm} \times$ $110 \mathrm{~mm} 16 \mathrm{~s} . \mathrm{w} . \mathrm{g}$. aluminium) should prove to be quite adequate. Happily, with this component, there is no need for an insulating washer but a liberal application of silicone grease is recommended before assembly. For most practical pur-

| TR1 | $\left\{\begin{array}{l}\text { c } \\ \text { b } \\ \text { e }\end{array}\right.$ | $\begin{array}{r} -28.4 \mathrm{~V} \\ 0 \mathrm{~V} \\ +0.6 \mathrm{~V} \end{array}$ |
| :---: | :---: | :---: |
| TR2 | $\left\{\begin{array}{l}c \\ b \\ e\end{array}\right.$ | $\begin{array}{r} -28.4 \mathrm{~V} \\ 0 \mathrm{~V} \\ +0.6 \mathrm{~V} \end{array}$ |
| TR3 | $\left\{\begin{array}{l}c \\ b \\ e\end{array}\right.$ | $\begin{array}{r} +0.6 \mathrm{~V} \\ +20.8 \mathrm{~V} \\ +21.4 \mathrm{~V} \end{array}$ |
| TR4 | $\left\{\begin{array}{l}c \\ b \\ e\end{array}\right.$ | $\begin{array}{r} -1.0 \mathrm{~V} \\ -28.5 \mathrm{~V} \\ -29.2 \mathrm{~V} \end{array}$ |
| TR5 | $\left\{\begin{array}{l}c \\ b \\ e\end{array}\right.$ | $\begin{aligned} & +1.0 \mathrm{~V} \\ & -0.5 \mathrm{~V} \\ & -1.0 \mathrm{~V} \end{aligned}$ |
| TR6 | $\left\{\begin{array}{l}\text { c } \\ b \\ e\end{array}\right.$ | $\begin{array}{r} +29.2 \mathrm{~V} \\ +1.0 \mathrm{~V} \\ 0 \mathrm{~V} \end{array}$ |
| TR7 | $\left\{\begin{array}{l}c \\ b \\ e\end{array}\right.$ | $\begin{array}{r} -29.2 \mathrm{~V} \\ -1.0 \mathrm{~V} \\ 0 \mathrm{~V} \end{array}$ |

All test voltages measured with a 20 k ohm $/ \mathrm{V}$ multimeter.

## Table 2. Test voltages

poses the rectifier heatsink can simply be provided by the external case or chassis of the equipment. This expedient will. however, not normally apply to the output transistors unless the case is specially designed with heat sinking in mind!

When the p.c.b. wiring is complete, the underside of the board should be carefully checked for solder bridges and dry joints, whereas the component side should be examined, paying particular attention to the correct placement and orientation of polarised components.

Connections to the heatsink mounted components (TR6, TR7 and REC1) and reservoir capacitors (C9 and C10) should be made by short lengths (typically not more than $150 \mathrm{~mm})$ of $16 / 0.2 \mathrm{~mm}\left(0.5 \mathrm{~mm}^{2}\right)$ stranded pvc covered wire. A typical wiring layout is shown in Fig. 4.


Internal view of the Power Amp

## INITIAL TESTS AND SETTING-UP

Before connecting to the mains supply and switching 'on' it is important to observe the following procedure:-

1. Adjust VR1 and VR2 so that they are both in the fully clockwise position.
2. Switch S1 to d.c. and temporarily short-circuit the signal input connector, SK 1.
3. Connect the loudspeaker for dummy load described next month). The loudspeaker should have an impedance in the range 40 hm to 160 hm and should be rated for a continuous power dissipation of 50 W .
4. Switch 'on' and measure the positive and negative supply rail voltages. These measurements can be most conveniently made using the terminal voltages developed across C9 and C10, respectively. The supply rail voltages, in the quiescent state, should be in the range $\pm 27 \mathrm{~V}$ to $\pm 30 \mathrm{~V}$. If the voltages differ appreciably, or if FS1 blows on switching 'on', the wiring


## 



INPUT

output


POWER

of the transformer and bridge rectifier should be carefully checked.
5. Switch-off and disconnect from the mains supply. Temporarily insert two 100 hm 1 W resistors in place of FS2 and FS3. This can be done quite simply by trimming and folding back the leads of the resistors so that the body of the resistor is gripped firmly by the fuse clips whilst electrical connection is achieved without the need to solder.
6. Transfer the d.c. voltmeter to the output terminals, SK2 and SK3. Reconnect the mains supply and switch 'on'. Adjust VR1 for exactly OV. If the adjustment has no effect or if the resistors get hot, carefully check the p.c.b. and wiring to the output transistors.
7. Switch 'off' and transfer the d.c. voltmeter to the


10ohm resistor fitted in place of FS2. Switch 'on' and adjust VR2 to produce a reading of 0.2 V . Check that a similar reading is obtained across the 10 hm resistor fitted in place of FS3.
8. Switch 'off' and disconnect from the mains supply. Replace FS2 and FS3 and remove the shorting link from SK1. Finally, select normal operation by switching S1 to the 'a.c.' position.

This completes the setting-up procedure and the amplifier is now ready for use. It is advisable to check the adequacy of the heat sinking arrangements by observing the temperature rise of the output transistor after, say, 15 minutes continuous operation at a reasonable output level (i.e. 10 W or more). If the rise in temperature is more than 25 deg.C above ambient, the heatsinking should be improved

NEXT MONTH: We shall provide constructional details of a 100 W dummy löad and a simple preamplifier/line driver.

# Spectrum DAC/ADC Board <br> R.A.PENFOLD 

WITH something like a million ZX Spectrum computers now in circulation there are, no doubt, a great many in the possession of electronics enthusiasts who would like to use them in computer based measurement and control applications. One of the $Z \times$ Spectrum's main shortcomings is a lack of built-in interfaces, and there are no ports ready fitted to the machine that are suitable for applications of this type. However, it is quite easy to fit interfaces onto the expansion port, and an analogue interface is one of the most useful from the electronics enthusiasts' point of view.

The port featured in this article gives both analogue-todigital and digital-to-analogue conversion. Both have 8 bit resolution, which is more than adequate for most practical applications. The analogue output has an output voltage range which is adjustable from 0 to 2.55 volts to about 0 to 10 volts, but with additional circuitry the output voltage range could easily be converted to any desired span within reason. The analogue input has adjustable sensitivity, with the full scale value variable from 2.55 volts to about 25 volts. Again, with suitable additional circuitry practically any input voltage range could be accommodated. The maximum rate of conversion is guaranteed to be no less than 66000 per second, and in most cases in excess of 100000 per second can be achieved. Even the guaranteed rate is fast enough for most high speed applications such as digitising audio signals.

## SYSTEM OPERATION

The block diagram of Fig. 1 helps to explain the overall way in which the unit functions. The digital-to-analogue converter is the more simple of the two converters. This consists basically of a precision 2.55 volt reference source, a resistor network (known as an R-2R network) and eight electronic switches. The electronic switches are controlled by the eight


Fig. 1. Block diagram
digital inputs, and when activated they connect the precision reference source through to the output via some or all of the resistors in the R-2R network. Things are arranged so that each input, when set high, causes the output to be incremented by the appropriate amount. The operation of this type of converter has been covered in past issues of this magazine, and will not be considered in more detail here.

In order to drive the DAC from the data bus of the Spectrum an 8 bit latch is needed, so that data written to the converter can be stored in the latch and used to drive the inputs of the converter. The converter then gives a continuous output, and ignores signais on the data bus that are intended for other devices. The converter used in this project has a builtin data latch, and it can therefore be fed direct from the computer's data bus. An address decoder circuit provides the latching pulse when data is written to the converter

The DAC has a 2.55 volt reference source, which sets the maximum output voltage at the same figure. This gives a nominal 0 to 2.55 volt output range in 10 millivolt 10.01 volt) steps. A variable gain amplifier enables higher maximum output voltages to be obtained, up to a maximum of a little over 10 volts. Of course, with a higher maximum output voltage there are still only 256 different output levels, and the output increments in steps of more than 10 millivolts. However, for most applications, such as motor speed controllers and even audio applications, the resolution of an 8 bit converter is at least adequate. The amplifier gives the unit a low output impedance, but without additional buffering output currents of no more than a few milliamps should be drawn.

The analogue-to-digital converter is of the successive approximation type. This incorporates a digital-to-analogue converter which is driven by a fairly complex control logic circuit. The eight outputs of this control circuit constitute the


## COMPUNING PROJECT

output of the $A D C$. The output of the DAC is fed to one input of a comparator, and the input signal is fed to the other input of the comparator. When a trigger pulse is received at the "start conversion" input the most significant bit is set at one, but the other bits are all set at zero. If the output from the DAC is at a higher potential than the input signal the most significant bit is left at one, otherwise it is reset to zero. On the next clock cycle bit 6 is set to one, and, as before, it is either left at one or reset to zero depending on whether or not the output of the DAC is at a higher voltage than the input signal. On the next clock cycle bit 5 is set to one, and the process is repeated with this bit. In fact the same process is used for all eight bits, and at the end of this procedure the 8 bit binary number fed to the DAC is a valid digital representation of the input voltage. This method is reasonably fast, with the conversion taking no more than nine clock cycles, but successive approximation converters are reasonably inexpensive.


Fig. 2. Circuit diagram of the DAC/ADC board

The device used in this project does not have a built-in clock oscillator, and a simple C-R oscillator is used to provide the clock signal. The "start conversion" pulse is provided by the address decoder. The converter provides its output via an 8 bit buffer which has three-state outputs, and it can therefore be connected direct to the Spectrum's data bus. The "enable" pulse for the outputs is obtained from the address decoder, but an inverter is needed to give a signal of the right polarity. The converter has a nominal full. scale sensitivity of 2.55 volts, but a variable attenuator at the input of the unit enables this to be reduced somewhat if required.

## CIRCUIT DESCRIPTION

The full circuit diagram of the Spectrum Analogue Board appears in Fig. 2.

All the address decoding is carried out by IC3 which is a 74LS138 3 to 8 line decoder. The Spectrum has a Z80A microprocessor, but it uses a non-standard method of input/output mapping. The general scheme of things is to have the address lines normally high, with one of the lower lines being taken low to activate an input/output device. Some of the upper address lines are occasionally used to provide additional information to an input/output device. This leaves address lines A5 to A7 free for user add-ons. In this case A5 and the IORQ lines are fed to the negative enable inputs of IC3, and A5 must be taken low when reading from or writing to either section of the port (the IORQ line automatically goes low when a BASIC IN or OUT instruction is used).

The three main inputs of IC3 are fed from the read (RD) and write (WR) lines plus address line A6. This gives four usable outputs from IC3, two when reading and two when writing (four outputs are always high since the read and write lines never go low simultaneously). This is adequate for our purposes as only two write outputs and one read output are needed in this application. When writing data to the DAC the instruction OUT 65439, $X$ is used, where $X$ is the value written to the converter. This takes the write and $A 6$ lines low while the value written is present on the data bus, giving an output pulse from output 2 (pin 13) of IC3. Other addresses can in fact be used, but it is best to use 65439 as this places the address lines apart from A5 and A6 high, so that unwanted operation of any internal input/output circuits is avoided.

IC1 is the DAC device, and this is the popular Ferranti ZN428. It has an integral 2.55 volt reference source, but this requires discrete load resistor R1 and decoupling capacitor C1. IC4 is an ordinary operational amplifier non-inverting mode circuit, and this amplifies and buffers the output of IC1. VR1 enables the closed loop voltage gain to be varied from unity to about 5 or so, but in practice the +12 volt supply used for IC4 limits the maximum output potential to about 10 or 11 volts. VR2 is the offset null control, and this is adjusted to trim the minimum output voltage of the unit to zero volts.

The ADC- is based on IC2 which is a Ferranti ZN427. Like the ZN428, this has a built-in 2.55 volt reference source which requires a discrete load resistor and decoupling capacitor (R3 and C2 respectively). R1 is part of the high speed comparator, and this is fed from a negative supply so that comparator will respond properly to voltages right down to zero volts. R7 biases the input of IC2 to the earth rail and VR3 plus R5 are.used to provide a small. positive bias which gives improved accuracy at low input voltges. VR4, together with the input resistance of the circuit, acts as a variable attenuator.


Fig. 3. Component layout of the p.c.b.

## COMPONENTS

| Resistors |  |
| :---: | :---: |
| R1 | 68k |
| R2, R3 | 390 (2 off) |
| R4 | 22k |
| R5 | 820k |
| R6 | 2k2 |
| R7 | 8 k 2 |
| VR1, VR4 | 100k 0.1 W hor. pre-set (2 off) |
| VR2 | 10 kO .1 W hor. pre-set |
| VR3 | $1 \mathrm{M} \mathrm{O.1W} \mathrm{hor}. \mathrm{pre-set}$ |
| All fixed resistors are 0.25W 5\% carbon |  |

## Capacitors

C1, C2
$2 \mu 263 \vee$ radial elect ( 2 off)
C3
1 nF carbonate
100 nF ceramic
Semiconductors

| IC1 | ZN428E |
| :--- | :--- |
| IC2 | ZN427E |
| IC3 | 744 ST138 |
| IC4 | LF351 |
| IC5 | $74 L S 14$ |

## Miscellaneous

Printed circuit board (502-02)
$2 \times 28$ way 0.1 inch pitch edge connector
8 pin d.i.l. i.c. socket
14 pin d.i.l. i.c. socket
Two 16 pin d.i.1. i.c. sockets
18 pin d.i.l. i.c. socket
Ribbon cable, wire, Veropins, solder, etc.

IC5 is a 74LS14 hex inverting Schmitt Trigger, but in this circuit only three sections of IC5 are utilised. One of these (IC5c) acts as the clock oscillator in conjunction with feedback resistor R6 and timing capacitor C3. IC5b merely acts as a buffer at the output of IC5c. The clock frequency is approximately 600 kHz , which is the maximum guaranteed clock frequency for the ZN427. However, with most devices a substantially higher clock frequency is quite acceptable, and where high operating speed is essential using a somewhat lower value for C3 to give a higher clock frequency of up to about 1 MHz should give satisfactory results.

The "start conversion" pulse is taken from output 6 (pin 9) of IC3, and is generated using the instruction "OUT $65503,0^{\prime \prime}$ (the value written can be any valid quantity since the pulse is obtained direct from the address decoder and not from the data bus). The port is read using the instruction
"IN 65503". This gives a negative pulse from output 5 (pin 10) of IC3, but this is inverted by IC5a to give the required positive pulse to IC2.

At least nine clock cycles must be allowed to elapse between sending the "start conversion" pulse and reading the port, to ensure that the circuit has had time to complete the conversion. There is no problem in BASIC since the slow speed of this language means that the conversion will always have been comfortably completed before the port is read. The situation is different when using machine code, and it may them be necessary to use a delay loop to prevent a premature reading of the converter from being taken. The ZN427 has an "end of conversion" status output, but no means of reading this have been included in this unit, and as
the length of time taken for a conversion is virtually constant a delay loop is a perfectly practical way of doing things.

The circuit requires $+5,+12$, and -5 volt supplies. These are all provided by the Spectrum from its expansion bus, and no other power source is required.

## CONSTRUCTION

The component layout of the printed circuit board is shown in Fig. 3. There are a number of link wires and it is probably best to fit these first. 22 s.w.g. tinned copper wịre is suitable for the links. None of the integrated circuits are MOS types, but it is advisable to use sockets for these, especially in the cases of IC1 and IC2 which are not the cheapest of devices. The integrated circuits do no all have the same orientation, so be careful to fit them onto the board the right way round.

Connection to the Spectrum is via a piece of 17 way ribbon cable about 0.5 metres long. It is unlikely that 17 way cable will be available, but it is easy to cut down a piece of 20 way cable to the required number of ways. Connection to the board should not prove to be difficult provided the end of each lead first has a small amount of insulation removed and is tinned with a small amount of solder. A 2 by 28 way 0.1 inch edge connector is needed to make the connections to the expansion bus of the Spectrum. Suitable connectors complete with a polarising key are now readily available. Fig. 4 gives connection details for the edge connector.

## ADJUSTMENT

Connect the unit to the Spectrum prior to switching on. The Spectrum should then operate normally - switch off immediately and recheck all the wiring if it does not.

Assuming all is well, adjust the DAC first. Set VR1 and VR2, at a roughly midway setting, and then type the followin'g command into the computer:-
OUT 65439,0
This should give a low output voltage from the unit, and by adjusting VR2 it should be possible to trim the outputipotential to precisely zero volts. Next type into the computer the command:-
OUT 65439.255


Fig. 4. Connection details for the Spectrum edge connector

An output potential of around 7 to 8 volts should then be obtained. By adjusting VR1 any desired maximum output voltage of between 2.55 volts and about 10 volts or so can be set. Repeat this procedure a couple of times to make sure that everything is set up as accurately as possible.

To check the ADC and facilitate its adjustment type in the following short test program:-

## 10 OUT 65503.0

20 PRINT IN 65503
30 GOTO 10
When the program is run it should return a series of very low readings ( 0 or 1 ). Set VR4 at maximum resistance (fully counterclockwise), VR3 at a midway setting, and connect an input voltage to the unit that is equal to the desired full scale value. This should be in the range 2.55 to 25 volts. Run the program and set VR4 just far enough in a clockwise direction to give returned values of 255 .
In order to adjust VR3 an input voltage that produces 5 millivolts at pin 6 of IC2 should be applied to the cirrcuit. In other words an input potential that is $1 / 510$ th of the full scale input voltage is required. VR3 is then adjusted to give a series of reading that (more or less) alternate between 0 and 1. It is not essential to carry out this procedure, and accurate results will be obtained if VR3 is simply set for about half maximum resistance.
 SWOP Brothers EP44 computer printer/ typewriter RS232 for oscilloscope. Mr. Simall, 8 Cherrytree Road, Chinnor, Oxon.
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PAL: information on PCBs making, from amateur and experts. A. Larry, 56 Becher Street, Derby DE3 8 NN
UK101 software for sale or swops. Send for list of programs. Mr. P. Hale, 31 South Road, Stourbridge, West Midlands DY8 3YA.
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## Outlook

- Everyone in business breathed a sigh of relief once the US presidential election was over. The two-year run-up is almost unbearable for its unsettling effect:

All indications, are that 1985 will be a good, though possibly hard year for the electronics industry. In 1983 the number of spmall companies starting up provided a net gain of 47,000 , The 1984 figures, not yet avallable, are expected to beat this record and there is no reason why 1985 should be worsé. A sighificant number of the new start-ups will, be in or associated with the electronics industry.

Foreign investment in the UK continues at a high level: The prolonged miners' strike was apparently seen overseas as a one-off out-of-character industrial relations problem and not typical of the 'new realism' in British jndustry. In any case no foreign companies would want to invest in coal mining and potential investors may be impressed by the relative ease with which British industry carried on through what was intended to be a crippling exercise.
Expansions and new starts planned last year will begin to take effect. If wé look at Scotland's Silicon Glen there are now nearly 300 electronics companies employing more 'than 40,000 people. Inward investment since the Locate in Scot/and agency was'founded in 1981 has now topped $\uparrow 1,000$ million, most of it finding its way into hign-tech projects. And suibstantial iqvestment is similarly going into other areas. Even so they will not create many new jobs, one recent estimate being for 10,000 in the electronics industry this year. - Intenșe competition in personal computers will force prices down so intending buyers, would probably profit by delaying purchase. Alternatively, prices could stabilise but the product improved in the classic "more-bits-per-buck" context. But despite all the difficulties it will still be possible to score well in the consumer market as proved by Alan Sugar's Amstrad whose pre-tax profits topped $£ 9$ million in its last financial year?

## Information Technology

Information Technology which seemed so novel (although hardly new) only three years ago has now become accepted as the norm and no more exciting than radio or television. Some pessimists are already saying that Britain has been losing ground in this growing sector of industry. Their fears are based on the, increase in imported equipmen't compared 'with indigenous production.

At the higher levels of the technique the Alvey programme is now gaining momentum. Two new major contracts were awarded towards the end of last year. One carries the painfully contrived acronym of ADMIRAL derived from. ADvanced Mega Internet Research for Alvey. The other is merely called the Speech Recognition Project.

The ADMIRAL contract is a $£ 3$ million joint venture peing coordinated by GEC Research Laboratories. Partners are University College, London, The University of Lon-. don Computer Centre and British Telecom Research Laboratories.
The system will-link local area networks (LANS) through a 'mega internet overlay' to produce a single large system of data networks. The key feature is to allow high speed intercommunication between dissimilar equipment. It appears to be a fe-jlg of part of the Project Universe programme originally initiated by the Department of Trade and Industry and later transferred to the Alvey Directorate.

The voice recognition project is funded with $£ 2$ million and is centred on British Telecom Research Laboratories with collaboration from Cambridge University and Logica. Although most schoolchildren are acquiring keyboard skills it is also recognised that speech is the most natural form of communication between people and the same applies between people and computers.

Present voice recognition systems are primitive and generally respond only to single-word voice commands. It is hoped to expand into true verbal, dialogue between person and computer so that anyone who can talk can, for example, find what is 'required from' a data base without necessarily having any keyboard skill.

## Time for Schools

It is heartening to see that schools are .now to be networked through The Times Network for Schools (TTNS) which will give any school access to more than 200,000 pages of information by the end of the year. Secondary schools of which there are 6,500 will be first to join, followed by27,000 primary schools.

Future plans exist to network British schools to those on the continental mainland. Joining the network will be optional but the fees are modest and the scheme should prove popular and exciting.

Then we have the proposal for a university devoted entirely to information technology. It has the backing of a host of leading electronics companies but students
will have to pay fees to make the university self-financing.

Fears have already been expressed by egalitarians that the university will be antisocial because it will create an elite of the already advantaged who can afford the fees. Nonsense, of course. We need more, not less, centres of educational excellence.

## Improvisation

1 remember at a press conference organised by a Ministry of Defence electronics establishment asking how we would get on in a real war when the time scale of equipment development stretched over a period of years even when the equipment was comparatively simple. I had in mind the very few weeks which elapsed in 1940 between the alarming discovery that the Germans were using magnetic mines, and the countermeasute (degaussing of ships) devised and implemented. And this was only one example of many rapid developments of that war.

1 contrasted this with over 10 years of development of the Clansman radio system before it came into service. I was not very impressed with the reply which was more or less that we would probably muddle through as we always had done in the past.

My confidence has now been restored (well, almost) by Alfred Price in his new book 'Harrier \& Sea Harrier at War', published by Ian Allan Ltd. In it he describes 'Blue Eric', an electronic countermeasure system needed urgently for the Falklands war. If Harriers were to be operationally successful in the South Atlantic they would need self-protection against Argentine radar installations.

The threat was evaluated from normal military intelligence which already had details of the characteristics of radar equipment in service with Argentine forces. Existing electronic warfare pods (e.g. for Tornadb and Buccaneer) were too large and heavy for the Harrier so it was decided to use elements of the Sky Shadow equipment and fit them in a modified gun pod which would meet the weight and size requirements as well as the Jamming capability.

Marconi Defence' Systems were prime contractors and completed the design, testing and delivery of operational units, within 15 days instead of an estimated two years'at normal pace and at a quarter of the cost.

Blue Eric (named after its MOD project officer Squadron Leader Eric Annal) was never used in the Falklands. When the EWequipped Harriers arrived they were grounded for four days by bad weather and by the time they got airborne the conflict was virtually over, the Harriers then being used for front line ground attack where the radar threat was negligible or non-existent.
While it is comforting to know that the improvisational skills of yesterday have not been lost, one is still left wondering why an EW pod for Harrier was not already available and why, in peacetime conditions, equipment development times are so long and the "cos't so great.

#  The Principle and the Product <br> Tom Gaskell ba(Hons) ceng miee 

THE electronics industry is one of extremely rapid change. New products, ideas, and standards spring up continually, promoting a continuous state of flux and development. As a fairly young industry it is successful in discarding old and outdated principles in favour of newer, more beneficial ones; if change can be shown to be worthwhile in any specific situation, then that change is almost invariably made.
It comes as somewhat of a surprise, therefore, that for the production of documentation, text, correspondence, and computer programs, the primary means of interface between the human being and the machine is still a QWERTY keyboard. QWERTY is the standard layout of typewriter keys which was devised very many years ago with the principle intention of Slowing Down the typist to prevent jamming of the mechanism. In this age of mechanical sophistication and electronic keyboards the same requirement is no longer true since we can easily prevent jamming by other means. Hence, we are left with a legacy from a bygone age. The QWERTY layout is slow and complex to learn, with months of training being required before any proficiency is achieved. For many people such training is impractical, so they are reduced to 'two finger' typing, which is usually a slow and frustrating exercise.

## A NEWIDEA

When a company brings-forth a new idea for entering text into machines, it is bound to attract considerable interest. A few years ago a device called the 'Microwriter' appeared. It is a small, self-contained machine with only six keys, which is used with one hand only. The Microwriter company has been producing these devices in modest quantities ever since, and has recently started to advertise and promote the product in a more aggressive way, with various options and accessories now available.

## WHAT IS A MICROWRITER?

A Microwriter is no less than a battery powered portable word processor. It is just a little larger than a paperback book and has very few controls-some connectors, an ON/OFF switch, a liquid crystal display, and six keys. It is placed on a desk or held in the left hand, and typed on with the right hand. (As yet there isn't a left handed version since there would be problems connected with the way that the 'alphabet' of letter shapes are formed, as we shall see later.) The Microwriter can communicate over a bi-directional RS232 serial link with printers, full-sized word processors, computers, etc., and can store text either internally on battery backed-up RAM, or on any conventional external cassette recorder.

Characters or numerals are entered into the machine by pressing combinations of keys, rather than one key at a time as in the case of the QWERTY system. There are no markings on the keys since they can have different functions at different times, so the user is immediately forced into the excellent principle of touch typing, and looks at the display rather than at the keys being pressed. The user, therefore, has to learn all the sequences of keys to be pressed before being able to type correctly. This is the make-or-break aspect of the Microwritermany people are immediately put off by having to learn a potentially complex typing language. Fortunately, the people at Microwriter Ltd. have been very clever indeed in the choice of
keys to be pressed per character. The right hand is always held in the same place above the keyboard, one finger above each key, and the shape formed by the fingers pressing the keys bears a relationship with the shape, or some aspect, of the character which becomes entered into the machine. That relationship is sometimes obvious and direct, sometimes humorous, sometimes very corny, but inevitably is easily memorable. Fig. 1 shows some of these relationships, based on a slightly stylised layout of keys. The manufacturers suggest that they can be memorised in typically one hour, and certainly I have found this to be the case as far as friends, colleagues, and myself have been concerned. It is very easy indeed to learn to Microwrite; far, far easier than touch typing, and I have tried both!

## USING THE MACHINE

As each character is entered from the keyboard it is displayed on a single line liquid crystal display which can show up to 14 characters and two control symbols. The display acts as a 'window' on the text, and can be moved around within the text, either following new characters entered or to review what has already been written under the control of special commands. The text, as shown by the display, normally appears to shift to the left as each new character is entered by the keyboard and appears at the right hand end of the display. The sixth key on the Microwriter is a second thumb key, a little below the normal one, and it acts as a control key, allowing comprehensive control of the machine's functions. It is used either on its own, or with other keys in place of the normal thumb key. For example, entering the letter ' f ' (the First Four keys pressed), but using the control key instead of the thumb key, moves the display window in the text Forward one position; ' $\rho$ ' for Forward-it is corny, but it works! Doing the same thing with the letter ' $k$ ' moves the window backwards. In this case, ' $k$ ' stands for Korrect, so you use it when Korrecting errors!

## WILL THIS EVER REPLACE THE 'aWERTY' KEYBOARD?




Pressing the control key once, on its own, puts the Microwriter into upper case characters for just one entry, after which it reverts to lower case. Pressing it twice in succession, on the other hand, locks the machine into upper case continuously until the two thumb keys are pressed together to revert to lower case. The status of the machine is continuously shown by two control symbols in a yellow coloured area at the right of the display

Simple punctuation is provided as part of the normal lower case letter set, but more complex punctuation and numerals have to be accessed by a 'numerals shift' function. Entering the letter ' $n$ ', but with the control key pressed at the same time, shifts the Microwriter into the numerals mode for one character only; entering this combination twice in succession locks in the numerals mode, just like the upper case mode. There's another set of character/key relationships for the punctuation, with numbers being entered by a 'count on the fingers of one hand' type of technique. The requirement to shift for numerals is acceptable for word processing applications, but would make the Microwriter somewhat laborious for writing computer programs; for example.

To avoid timing problems when keys are pressed together, the Microwriter works on a key accumulation principle, and the character is only entered when all the keys have been released. Hence, you can start to press keys in any order, so long as at least one of them is being held down at any given time. When all the keys are eventually released, the result is as if all the keys that were depressed in that sequence, irrespective of their chronological order, were pressed simultaneously. This makes the keyboard action very 'forgiving', and allows characters to be entered very slowly and deliberately when required. The speed which can be obtained after only a few weeks' use is very high not as fast as touch typing, but certainly up to twice as fast as handwriting.

## EDITING AND WORD PROCESSING

When text has been written it can be edited (both deletion and insertion) and reviewed by appropriate use of the control key. To read through the written material, the user has to Jump back to the beginning (control $+j$ ) then scroll Forwards (control on its own, followed by control +f ; this then moves the display window along the text one word at a time, at a user selectable slow or fast rate, until you tell it to stop. The machine automatically enters 'carriage returns' at the end of each line, and ensures that these are between words, not in the middle of them. Via the control key the user can access tabulation, margin indents, document markers, page separators, alter line length, and do many other complex word processor functions. These become very difficult to memorise, and even more difficult to implement, and I would have thought that they would have only limited usefulness to most people.

The control key is also used to suitably configure the RS232 link. Although this can be used to load text into the Microwriter, its primary use is to transmit text to a computer, word processor, or printer from the Microwriter. Full handshaking is provided, and there are user selectable baud rates, data lengths, etc., so it will interface with most RS232 based systems. All settings and text are stored in RAM with battery back-up, so nothing is lost when the power is turned off. The machine even turns the power off itself if it is not used for a few minutes, to

Microwniber

## ALPHABET RECOMMENDED LEARNING SEQUENCE



Fig. 1. Sometimes corny; but inevitably memorable
conserve battery life. The batteries are rechargable types, and a suitable charger is provided with the machine. Up to 1600 words, or typically 5 pages of A4 size, can be stored in the memory of the machine. (Much more if cassettes are used.)

## THE HARDWARE

The packaging of the Microwriter inspires confidence! It is housed in a very solid injection moulded plastic case. The keys are ultra-low activațing-forçe microswitches with moulded keys. Their action is light but positive, and their positioning is ergonomically spot-on. Inside there is just one main p.c.b. holding the RCA CDP1802A CMOS microprocessor, four HM6116 CMOS 2k Byte static RAMs, and a 2564 8k Byte CMOS EPROM, along with an 'intelligent' liquid crystal display above it as a sub-assembly, and other assorted CMOS i.c.s. The batteries are housed between the microswitches in the upper half of the case. It's a well laid out and professionally built product.

With the Microwriter itself comes a good quality soft carrying case, a battery charger, a cassette recorder connecting lead, some 'crib cards' giving a quick reference to control codes, characters, punctuation, etc., and two instruction manuals; a new user's guide, and a more complex systems manual for setting up communications protocol and the like. The new user's guide is effectively the main instruction manual for the machine, and without doubt is the best manuat that I have seen for a piece of consumer electronics. The cartoon characters used might annoy some, but they will drive the points firmly home to just about anybody, whatever age or ability. Other product manufacturers would do well to study this manual and compare its high standards with their own!

There is an optional television interface unit available for the Microwriter which I'm somewhat less happy with. It interfaces to the RS232 port, and allows the display of text on a domestic television set or a composite video monitor. It is expensive (around the $£ 100$ mark) and gives very limited facilities. Writing onto the screen as you enter text works reasonably well, but if you just want to dump a letter, for example, onto the screer, to check its layout, the use of the Microwriter becomes somewhat more contrived. It's very difficult to put a letter onto the screen without the top of the letter scrolling off the screen as soon as the bottom of the screen is reached. The unit that I tested also failed to get the ends of the lines correct when dumping onto the screen; parts of words were left at the end of some lines, then the whole word reappeared again on the next line. For the majority of potential Microwriter users I would question the necessity for the television interface unit-when you've got the hang of Microwriting you probably don't need it. It seems to be more suitable as a shared facility between several users, and generally seems to be somewhat of an afterthought rather than an integral part of the Microwriter system.

## THE OUINKEY

For many people, the cost of a Microwriter ( $£ 299$ plus VAT), although low by office equipment standards, is too high for them to consider it as a personal purchase. However, they could consider investing in a 'Quinkey'. This appears to be an ordinary Microwriter at first glance, but lacks most of the connectors and the display. In fact, it contains no electronics, just a set of microswitches and resistors which enables up to four of them, ingeniously, to plug into the analogue inputs of a BBC microcomputer. For just under $£ 50$ the full Quinkey package provides good value, consisting of the the Quinkey itself, a manual, some crib cards, a connecting lead, and the software to run the system. Further Quinkeys on their own cost around $£ 30$.

The software enables the Quinkey to be used as well as the standard BBC QWERTY keyboard, not only with software within the BBC micro such as BASIC, the Acorn DFS, etc., but
also with software packages such as Wordwise and similar. A version for the Spectrum is soon to be made available, and Microwriter are working on versions for other popular personal computers too. All this helps to bring the unique qualities of Microwriting to the private individual, schools, colleges, etc.

## APPLICATIONS—WHO USES IT?

The most obvious market for the Microwriter is with professionals on the move-salesmen, executives, engineers, and anybody who does an amount of documentation, report writing, letter writing, etc. On the train or 'plane they can write their meeting reports, or they can keep notes in the field or by their work benches, and either print the results out so that they are legible to themselves and to their colleagues, or if necessary dump them onto the office computer or word processor to be tidied up before final printing. There's no duplication of effort, the typists no longer having to work from handwritten notes.

The small size, portability, and ease of use of the Microwriter are attractions which a QWERTY keyboard has never had. Microwriting can never be as fast as good touch typing, so it will not be used to replace QWERTY keyboards in typing pools or secretarial offices, but for thousands of unqualified typists it offers a refreshing 'alternative to the two-fingered struggle, so it should be of great interest to small businesses, the police, sales personnel (especially those working from home), budding novelists, and even to the writers of magazine articles! For schools it has the advantage of allowing the connection of four Quinkeys to each BBC microcomputer, which immediately shares out normally limited resources to many more children If accepted for these applications, it can only help establish Microwriting as a world-wide standard in' years to come.

## THE FUTURE OF MICROWRITING

Until recent months the promotion of the Microwriter was a very low-key process, although some rather more prominent advertising is now being seen. Oyer 7000 have been sold, which can only be the very tip of the potential iceberg. I must express reservations, however, about the approach that Microwriter are making on the market place, which seems to be rather uncertain and lacking in self-confidence. I first saw a Microwriter 'in the flesh' in the latter part of 1983, when I had a demonstration and a loan from a distributor for' a couple of weeks. I expressed a great interest when I returned the machine to him, and was promised more information and a follow-up call shortly. I néver heard from him, or another distributor I contacted, ever again. At the end of January 1984 I approached Microwriter themselves for information and a review sample to help, prepare this article. I also ordered two Quinkeys for my own use. I am writing this article in mid August; the review sample only arrived three weeks ago! The Quinkeys arrived in the middle of June, some 19 weeks after they were ordered, and only after telephone calls at the rate of once per fortnight for most of that period. I persevered-I wonder how many others did not?

I hope that the future is very rosy for Microwriting. Amongst friends and colleagues the Microwriter has created more interest than any other piece of equipment that I can remember. The concept of the Microwriter is a work of genius. The market is potentially vast, the product works, well, and the presentation is superb. The price is a little high, but should not deter the professional market, with the lower cost market being satisfied by the Quinkey: Let's just hope that Microwriter can improve on the delivery and planning side of it, put some more aggression into the marketing, and produce a commercial, not just a technical winner. What a great shame it would be if the Microwriter concept was lost to an overseas supplier, as has happened to so many other viable products from the UK.

More information can be obtained from Microwriter Ltd;, 31 Southampton Row, London WC1B 5HJ. (01-831 6801).

## DIGITISATION

Everyone talks about the information explosion. The key is digitisation. With digital telephone systems what goes down the line is a series of PCM pulses, rather than analogue waves. Once you have that situation, the sky's the limit.

PCM pulses can carry telephone quality speech, high quality stereo radio, TV pictures, computer data, teletext, viewdata; in fact any information that can be converted into an electrical signal. Switching is by microchip, instead of the primitive Strowger electro-mechanical relay which phone systems have used for the best part of a hundred years.
By interieaving different calls in the same data stream, the capacity of a link goes up around 15 times, i.e. a pair of copper wires that normally carry one analogue telephone call, can carry fifteen digitals. With optical fibres, and the signals carried as light pulses rather than electrons, capacity rises much, much higher.
The British Post Office started working on PCM phone links 20 years ago. Few people know that the PO installed an experimental digital exchange at Earl's Court in 1968 and had it running until 1975: That was when talk about System $X$ started.
Cynics say that the System was called $X$ because no-one really knew what it was going to do or how it was going to do it. Essentially it's a computer switching service for PCM streams and there are now six System $X$ exchanges working in London. One is at Baynard House in the City of London. The first five were prototypes.
Once data streams are digitally switched and connected, the options available open up wide. There is no problem in providing conference calls, automatically re-directing calls to other numbers or displaying the telephone number of origin when you receive a call.

## ELECTRONIC MAIL

Already many people in Britain are using electronic mail, which is a hybrid system of sending digital data down an analogue telephone line. I'm one of them and there are quite a few stories to tell about how the system works in practice, as opposed to theory!

More of that in a future month. At the moment I am trying to find out why the main computer used by Telecom Gold for electronic mail keeps going wrong and leaving users like me stranded!

Why worry about information technology? There's a very short answer. It is always far cheaper to send electronic data down a telephone line, or over a wireless link, than shift people or bits of paper from town to town or country to country.

The best example of this is what happens at the Economist magazine. This Londonbased publication also prints in America and the Far East. Printing master plates are sent by airline courier to the Orient. Until a year ago they were also sent to America.
The plum job on the Economist was to take a day trip on Concorde to New York and back, with the print plates, for safe keeping. Now the magazine text is converted to digiţal data and sent by satellite direct to a Connecticut printing works, which publishes virtually simultaneously with London.

Wisely the Economist still sends a back up text by 'plane just in case the satellite link breaks down. But no-one gets the plum job of going along with them any,more.

## VIDEO NEWS

Polaroid has joined Kodak in 8 mm video. Sony may follow next year but so far everyone else is sticking with their existing VHS and Beta formats. Ironically by joining Kodak, Polaroid may well have helped its rival succeed. The extra name gives the new format credibility.

At the Chicago Consumer Electronics Show both companies were demonstrating NTSC camcorders using the 8 mm cassette. Picture quality was good and sound, using f.m. mono, seemed OK. The big question mark is over tape supply.
Video writing speed is very low; 3.8 metres a second for NTSC and 3.1 metres a second for PAL and SECAM. So packing density must be very high. You can get it either from tape coated with metal powder (MP) and coercivity around 1600 oersted. But this needs video heads which are expensive and may be short lived. The other way is to use lower coercivity tape coated by evaporation of cobalt-ferric metal in a vacuum (ME). No one has yet succeeded in making ME tape reliably in bulk.

Kodak started shipping 8 mm camcorders to US traders last September. A 90 minute cassette costs $\$ 24$ and the system $\$ 2000$. There is no sign yet of a PAL or SECAM prototype. Although 8 mm video almost certainly comes too late and too expensive to catch the domestic market, it could well form the basis of a new professional camcorder format.

Sony has both domestic and pro interests. Kodak and Polaroid are paying Matsushita, Toshiba and TDK to get the technology right for domestic use. Professional use is the logical follow on.

## CLEAN CUT

I have now seen inside several compact disc and videodisc manufacturing plants in Britain, Germany and Japan. They all have one thing in common with a microchip factory, that is absolute cleanliness.

Exactly the same situation exists in magnetic tape factories, where any dirt in the atmosphere will end up as nonmagnetic blemishes in the coating and cause dropout.
Air in the so-called "clean areas" is filtered to Class 100, that is to say less than 100 particles of less than 0.5 micron size in every cubic foot of air. The pressure of air inside these clean areas is higher than the atmosphere outside, so when a door opens clean air blows out and dirty air leaks in.
The staff must wear full length lint-free jump suits, like space clothing, and only a few visitors are allowed in. Usually there is an air shower, where blasts of clean air flush dirt, dust; dead skin and dandruff off every human passing through.
If only, I think every time I visit one of these plants, factories which press ordinary records would take even remotely comparable steps to preserve cleanliness. The official answer is that it's not necessary.

Certainly, by comparison, the technology of LP production looks like a blunt instrument. But it is easy to forget that a vinyl LP record is by far the most precise product mass produced from plastics!
The groove of an LP record is specified by IEC standard to be never less than 25 microns (or millionths of a metre) wide and preferably not less than 35 microns wide. As a "yardstick" a human hair is around 50 microns in width. The IEC puts stylus tip radius at between 15 and 18 microns.

Now let's look at a Laservision videodisc, and a compact dise digital audio record. Both have a spiral of information pits with a track pitch of 1.6 microns.

For videodisc the pits are 0.5 microns wide, and for compact disc they are 0.6 microns wide. Video pit depth is 0.1 micron and CD depth 0.12 microns.
In other words there is very little difference in the dimensions; both are at least 50 times smaller than the LP groove. The laser spot for videodisc playback is focused to a circle of 0.9 micron diameter and for compact dise it is 1 micron: The layer of protective lacquer in a compact disc has to be exactly 1.2 millimetres thick, or jit will 'affect the laser focus.

## PARTY TURN

If you collect useless information to bring out of the bag at boring cocktail parties, here's one for the bag. A CD player rotates the disc at a speed which varies between 3.5 revolutions a second and 8 revolutions a second, to give a constant tracking velocity of 1.25 metres a second.
That means that for a one hour disc there are 4.5 kilometres of track on a single side. For a laser videodisc the track length is 31 kilometres

BARRY FOX

## TERMS OF BUSINESS

* All prices exclude V. A T. and carriage. Please add carriage to order total before adding V.A.T.
* Carriage charges extra on all orders as follows: Components
Books/Data/Software
£2.00
Printers, Monitors, Disc drives, etc
E4.50
* Strictly cash with order or credit card (Access or VISA) only.
* Delivery is normally from stock but please allow up to 28 days.
* Any query or complaint regarding an order should be made in writing within 7 days of receipt of the
order. No telephone queries will be entertained
* Goods incorrectly ordered cannot be accepted for replacement without our prior agreement. Due to high processing costs, a minimum of $15 \%$ handling charge may be levied on any returns or cancelled orders

We will issue a full immediate refund, if requested for out of stock items

* All items carry full manufacturers warranty
* A VA T receipt will be supplied with all orders.
* Prices quoted are correct at the time of going to press but we reserve the right to effect changes without prior notice.




# SEMICONDUCTOR  

## POWER OP-AMPS (TCA365 and TCA2365)

ONE of the most important components available to the analogue circuit designer is the operational amplifier, or 'op-amp'. The majority of these, however, are somewhat limited in their load driving capabilities. Simple devices such as the 741 can only output 25 mA under short circuit conditions, or 10 mA in normal operation. For much higher currents it is usually necessary to add extra driving transistors to a conventional op-amp.

The TCA365 and TCA2365 are power opamps which allow the designer to use a single i.c. in high power applications rather than the more cumbersome 'op-amp plus components' approach. In practice, they behave as fairly ordinary op-amps with the exception that their output stages can drive up to 3 amps in the case of the TCA365, or 2.5 amps per amplifier in the case of the dual op-amp TCA2365. The two i.c.s are very similar, with both sets of specifications being given in Fig. 2. The main points to watch are supply voltage maxima, output currents, and power dissipation; these all vary between the 365 and the 2365. (Note that the output current shown for the TCA 2365 is 2.5 A per amplifier, not for the whole i.c.) Fig. 1 shows the pinouts of the i.c.s. For moderate to high power applications, heatsinks should be used. These should be insulated from the i.c.s' tabs if the internal connections to the -ve supply could cause short circuits or problems.
The TCA2365 has an 'inhibit' input which can be used to turn the outputs of the op-amps off, ie. high impedance (approximately 4 k ). Inhibiting is effective when pin 6 is taken to the -ve supply rail, and the amplifiers operate normally when pin 6 is taken above 3.0 V referred to the -ve supply, or left unconnected. Both the TCA 365 and the TCA 2365 have extensive protection; they are d.c. short circuit proof and have thermal overload and safe operating area protection. The internal current limiting makes them ideal for driving complex loads, and especially for driving filament lamps, whose low resistance in the 'cold' state can cause problems with other types of driver.

## BASIC CIRCUITS

Some basic circuits for use with these power op-amps is shown in Fig. 3. In all cases there is an external Zobel network (sometimes known as a Boucherot network) fitted between the output and 0 volts to help to maintain stability under widely varying load conditions.

The 1 ohm resistor does not have to be high power ( $\frac{1}{3}$ watt will do) and the capacitor must be 100 nF for the TCA365, or 220 nF for the TCA2365. It is unimportant which way up the network is fitted; the capacitor can be connected to 0 V and the resistor to the output, or vice versa. Both power op-amps can be used with either split or singie rail supplies, just as would be possible with most conventional op-amps.
Figs. 3a and 3c are very straightforward conventional op-amp circuits, and apply perfectly weil to the TCA365 and TCA2365. For minimum offsets, $\mathrm{R}_{\mathrm{g}}$ in Fig. 3a and $\mathrm{R}_{\mathrm{i}}$ in Fig. 3 c should be included as shown, although in many circuits these are unnecessary and can be replaced by short circuits for economy. Both these circuits, however, should really only be used for higher gain circuits; +10 dB or more, or preferably +20 dB . For lower gain circuits, and certainly for anything less than 10 dB (approximately $\times 3$ ), the configurations of Figs. 3b and 3d should be used. For unity gain, use typically between 10 k and 100 k for both $R_{i}$ and $R_{f}$, with $R_{0}$ approximately one tenth of that value, in Fig. 3b, and typically between 10 k and 100 k for $\mathrm{R}_{\mathrm{f}}$ in Fig. 3d, with $\mathrm{R}_{\mathrm{o}}$ one tenth of that and $\mathrm{R}_{\mathrm{g}}$ an open circuit. The reason for all this is concerned with The rea
stability. stability.

## STABILITY

There are many factors influencing stability in operational amplifiers. These tend to be involved, complicated, steeped in complex-plane mathematics, and certainly beyond the scope of Semiconductor Circuits! Empirically, most electronics engineers and enthusiasts learn some straightforward rules of thumb about how to keep amplifiers stable and prevent problems of self-oscillation at several megahertz. A common 'cure-all' is to connect a small value capacitor, typically less than 100 pF , between the output and the inverting ( -ve ) input. Don't do this to a TCA365 or 2365 ! Even if it doesn't actually cause oscillation (which it probably will) it will certainly make oscillation much more likely. This is basically due to the fact that the opamps have poor stability at low gains, and a capacitor across the feedback loop ensures low gains at high frequencies. For gains of more than $20 \mathrm{~dB}(\times 10 \mathrm{gain}$ ) the i.c.s are normally quite stable, assuming that the Zobel network is fitted and that P.S.U. decoupling is taken care of. More than 10 dB ( $\times 3 \mathrm{gain}$ ) is normally acceptable, but below this there can be problems with transient responsse


|  |  | TCA365 | (Single 0 | p-Amp) | TCA2365 (Dual Op-Amp) |  |  |  |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| Characteristic | Notes | Minimum Value | Typically | Maximum Value | $\begin{array}{\|c} \text { Minimum } \\ \text { Value } \\ \hline \end{array}$ | Typically | Maximum Value | Units |
| Supply voltage | All spec's quoted at $\pm 15 \mathrm{~V}$ for TCA365 and $\pm 10 \mathrm{~V}$ for TCA2365 In normal operation: | $\begin{gathered} \pm 4 \\ *(\operatorname{or} 8 \mathrm{~V}) \end{gathered}$ | $\pm 15$ 20 | $\begin{gathered} \pm 18 \\ \left(\begin{array}{c} \operatorname{cor} 36 \mathrm{~V} \\ 40 \end{array}\right. \end{gathered}$ | $\begin{gathered} \pm 4 \\ *(\operatorname{or} 8 V) \end{gathered}$ | $\pm 10$ | $\frac{+13}{(\text { or } 26 \mathrm{~V})}$ | $\checkmark$ |
| Quiescent current | $\left\{\begin{array}{l}\text { In normal operation: } \\ \text { with amps inhibited: }\end{array}\right.$ |  | 20 | 40 |  | 30 5 | 50 8 | mA |
|  | (TCA2365 only) |  |  | - |  |  | 8 | mA |
| Temperature range |  | 0 |  | + 70 | -25 |  | +85 | ${ }^{\circ} \mathrm{C}$ |
| Maximum O/P current | Per amplifier |  |  | 3.0 |  |  | $2 \cdot 5$ | A |
| Maximum I/P voltage: | (Differential) |  |  | Supply rails |  |  | Supply rails |  |
| 1/P offset voltage |  | -10 |  | +10 | -10 |  | +10 | mV |
| I/P offset current-... |  | -0.2 |  | +0.2 | -0.1 |  | +0.1 | $\mu \mathrm{A}$ |
| Temperature coefficient | (Of input offset current) |  |  | 0. 1 |  |  |  | $n A /{ }^{\circ} \mathrm{C}$ |
| Input current |  |  | 0.2 | 1.0 |  | 0.25 | 1.0 | $\mu \mathrm{A}$ |
| Input resistance | At 1 kHz |  |  |  | 1.0 | 5 |  | $\mathrm{M} \Omega$ |
| Output voltage | Load resistance $=470 \Omega \quad$ at <br> Load resistance $=4.7 \Omega \quad 1 \mathrm{kHz}$ | $\begin{array}{r}  \pm 13.0 \\ \pm 11.7 \\ \hline \end{array}$ | $\begin{array}{r}  \pm 13.2 \\ \pm 12.0 \end{array}$ |  | +8.0 | $\pm 8.5$ |  | V |
| Slew rate |  |  | 4 |  |  | 4 |  | $\mathrm{V} / \mathrm{\mu s}$ |
| Voltage gain | Open loop, at 100 Hz |  | 90 |  | 70 | 80 |  | dB |
| 1/P common mode | Load resistance $=470 \Omega$ | +13.4 +15.0 | +13.5 +15.0 |  | +7.0 +10 | + 7.5 -10.5 |  | V |
| voltage range | Load resistance $=470 \Omega$ | -15.0 | -15.0 |  | -10 | $-10.5$ |  | $\checkmark$ |
| Common mode rejection ratio | Load resistance $=470 \Omega$ | 75 | 83 |  | 70 | 80 |  | dB |
| Supply voltage rejection ratio | Gain $=\times 100$, frequency $=20 \mathrm{~Hz}$ Gain $=\times 10$ frequency $=100 \mathrm{~Hz}$ | 50 | 62 |  | 70 | 80 |  | dB |
| Power dissipation | Total for package, at $90^{\circ} \mathrm{C}$ |  |  | 15.0 |  |  | 6.0 | W |
| Equivalent I/P noise | Gain $=\times 11,1 / P$ resistor $=10 \mathrm{k}$ |  |  |  |  | 3.0 |  | $\mu \mathrm{V}$ |
| Inhibit input | For i.c. turned off | - |  | - | 0 |  | 1.0 | V |
| (TCA2365 only) | For i.c. turned on | $\square$ |  | - | 3.0 |  | (+ve supply) | V |

Fig. 2. Specifications (note different supply rails used in measuring spec's.)
(overshoot of the output on square waves) and stability,

Hence, the circuits of Figs: 3b and 3d should be used for low gain applications. Although the actual voltage gains of these circuits are exactly the same as the equivalent gains of Figs. 3a and 3c, the inclusion of $\mathrm{R}_{\mathrm{o}}$ actually causes the op-amps to be working in a 'high gain' way. Normally, this is rather undesirable, since there is no apparent benefit to the user and the amplifier has a much noisier output voltage, but in this application the 'pseudo gain' helps to ensure stability at low real gains, and is to be recommended: for use with any circuitry demanding a gain of less than $\times 4$, or even less than $\times 10$ to be on the safe side.

## POWER SUPPLIES

The capabilities of these op-amps to dump several amps from the supply rails into a load puts considerable strain on the P.S.U.s used. The best general guidance that can be given is to consider the devices as audio power amplifiers, and to use the same constraints about removing earth loops, supply decoupling, keeping inputs away from outputs, etc. As with audio power amplifiers, the TCA365 and TCA2365 will overheat very rapidly when oscillating at very high frequencies, so any debugging of stability problems should be done very rapidly, and for short periods only! Specifically, it is good practice to take the 0 V connection to the feedback resistor, input resistors, input decoupling, etc, as appropriate, to the power supply as a separate connection from the load, Zobel network, etc, to isolate the input as far as possible from the output. In all cases, each power op-amp should have

GAIN $=\frac{R^{\dagger}}{R_{1}}$
FOR MINIMUM OFFSET. MAKE
DE564]

$$
R g=\frac{R_{i} \times R i}{R i+R_{i}}
$$



Fig. 3c. Non-inverting, high gain


Fig. 3d. Non-inverting; low gain

Fig. 3. Basic power op-amp circuits


Fig. 4. Simple sensor detector and switch
$100 \mu \mathrm{~F}$ capacitors between its supply rails and 0 volts, or simply across its rails in the case of single supply sysțems.

When inductive loads are to be driven, diodes should be connected between the opamp output and the supply rails, as shown in Figs. 4, 6 and 8. This protects the op-amp's driver transistors from the huge back e.m.f. spikes generated when inductive loads are suddenly turned off.

## APPLICATIONS

The uses for these i.c.s fall mostly into the realms of control and switching. They will amplify and drive audio signals, but not with the fidelity that can be achieved by audio power amplifiers specifically designed for the task. Essentially, these i.c.s are excellent for use on many occasions when an ordinary opamp simply runs out of drive capability. Some examples of switching applications are shown in Figs. 4, 5 and 6.

A simple sensor circuit is shown in Fig. 4 using the power op-amp as a comparator and directly driving relays 1 and 2 . The sensor can be any device which varies in resistance in


PE59M
proportion to a required effect. For example, a light dependent resistor (e.g. ORP12) or thermistor would allow the sensing of light level or temperature respectively. The sensor preset scales the voltage range produced by the sensor at the op-amps non-inverting input, while the threshold preset alters the level at which the op-amp changes state. $\mathbf{R}_{\mathrm{h}}$ provides some hysteresis to stop the op-amp 'hunting' or 'chattering' when the sensed value is just on the threshold point.

A square wave oscillator is formed by the power op-amp in Fig. 5. The mark/space ratio potentiometer adjusts the charge and discharge paths for $C_{T}$ such that their sum is always constant (i.e. the frequency does not vary) but the mark/space ratio can be adjusted over a wide range. The frequency itself is set by a combination of the value of $\mathrm{C}_{\mathrm{T}}$ and the setting of the 100 k 'frequency' potentiometer. This circuit is capable, by virtue of the power op-amp, of driving pulses of several
amps into any suitable load. Output diodes should be added, as shown in the other circuits, if the load is to be an inductive one.

## DIFFERENTIAL DRIVING

Finally, Fig. 6 shows two power op-amps driving a d.c. motor in a 'bridge', or differential drive mode. This allows the direction of rotation of the motor to be changed. IC1 and IC2 are arranged as comparators with $\mathrm{R}_{\mathrm{H}}$ and $\mathrm{R}_{\mathrm{L}}$ setting the threshold voitage $\mathrm{V}_{\mathrm{T}}$, and are designed to be driven by logic signals $\mathbf{A}$ and $\mathbf{B}$. If both inputs $A$ and $B$ are at a low level (logic 0 ), both sides of the motor will be at a low level ( 0 V ). If both inputs are high (logic 1), then both sides of the motor will be at a high level, near to the + ve supply rail. In both these cases the motor will not run, since there is no differential voltage across it-both terminals of the motor are at the same voltage. However, if one input is high, and the other low, the motor will run in one direction or the other. Normally, $\mathrm{V}_{\mathrm{T}}$ should be set to a suitable level for the logic family which is used to control IC1 and IC2; ideally, $\mathrm{R}_{\mathrm{H}}$ and $\mathrm{R}_{\mathrm{L}}$ should be taken from the logic's power supplies, not the + ve poweí supply as shown, to ensure accuracy of the threshold voltage.

The TCA365 and TCA2365 are ideal for use in controlling motors, relays, magnetic valves, and solenoids. They can also make a good basis for the design of regulated power supplies. Their current limiting makes them especially suitable for driving filament lamps and other unusual loads, and their op-amp configuration makes for easy interfacing of these loads with both analogue and digital circuitry. When stability is taken into consideration these are easy and effective to use, and provide an economic solution to many power driving problems. Both i.c.s are available from Electrovalue, 28 St. Jude's Road, Englefield Green, Egham, Surrey.

PE60M

| INPUTS |  |  |
| :---: | :---: | :--- |
| B | A | EFFEC T |
| 0 | 0 | STOPPEO |
| 0 | 1 | RUN CLOCKWISE |
| 1 | 0 | RUN ANTICLOCKWISE |
| 1 | 1 | STOPPEO |

Fig. 6. Bi-directional motor control

Fig. 5. Power pulse generator

# MICROPROCESSOR CONTROLLED DC MOTOR DRIVERS 

AST month we looked at a timer circuit - triggered by a microprocessor. This month we have another microprocessor based project, to allow the analogue driving of d.c. motors. Again, the circuit assumes the use of the Z 80 microprocessor, although it is very easily adaptable for other devices. The circuitry is shown in Figs. 7 and 8 and the Veroboard layout in Fig. 9. The circuit consists of two separate sections; the decodet, and the driver. Up to 8 drivers can be operated by one common decoder.

The address decoding is done in a similar way to last month's project. IC 1 compares the most significant nibble ( 4 bits) of the 8 bit port address with the settings of S1 to S4. Each switch is turned off to correspond to a logic 1 , and on for a logic 0 . The comparison is only enabled when both $\overline{I O R Q}$ and $\overline{W R}$ are at logic 0 (determined by IC5c), corresponding to the microprocessor performing an I/O write instruction. IC2 is a 3 -to- 8 line decoder used for the least significant nibble of the port address. Address line A3 must be held at logic 0 and the other 3 lines then provide the address of the driver circuit required. The least significant nibble of the driver address will therefore be $\emptyset$ to 7 , as determined by the latch output of IC2 used. The outputs of IC2 are inverted, and are wired to the LATCH inputs of any required driver circuits. Hence, if one particular driver circuit LATCH input was connected to LATCH output 3 of IC2, switch S1 was off and switches S2 to S4 were all on, that driver circuit would respond to address 13 H (i.e. 19 in decimal). Driver circuits can thus be provided at port addresses $\emptyset \emptyset \mathrm{H}$ to $\emptyset 7 \mathrm{H}, 1 \emptyset \mathrm{H}$ to $17 \mathrm{H}, 20 \mathrm{H}$ to $27 \mathrm{H}, 30$ to 37 H , etc.

IC3, with associated components, provides a 5 volt regulated supply. This can be omitted if the microcomputer's own 5 V supply is to be used to power the logic supply to the circuitry. IC4 provides a reference voltage which tracks the Vp power supply. This reference will be approximately 1.8 V for a 12 V supply.

## THE DRIVER CIRCUITRY

IC6 is a digital to analogue ( $\mathrm{D} / \mathrm{A}$ ) converter with a built-in data latch, which connects to the microprocessor's data bus. Data is latched in by the required output of IC2. IC7 is a TCA 2365 dual power op-amp which drives the motor differentially to provide both forward and reverse control from a single supply voltage. (It's based on an analogue version of the differential driver in Fig. 6). IC7a amplifies the output of IC6 and provides the positive output phase, while IC 7 b inverts this positive drive signal about a half-rail reference voltage set by R17, R18 and VR2, and provides the negative output phase.

When the output of IC 6 is at 0 V, pin 1 of IC7a is near to 0 V and pin 9 of IC7b is near to the + ve supply. When the output of IC 6 is at $V_{\text {ref, }}$ the reverse is true. When IC6's output is at half $\mathrm{V}_{\text {ref, }}$, both power op-amp outputs are at half the supply rail and the motor is stationary. Presets VR1 and VR2 aiter the gain and offset of the output voltages, and D1,


Fig. 7. Decoder circuit
a 'Bi-Colour' l.e.d., glows green for forward direction, red for reverse and turns off in the stationary condition.

The use of an 8 bit D/A converter allows 127 forward speeds and 127 in reverse, although it is unlikely that the electric motor in use will operate all the way down to OV. Note that $0 \mathrm{~V}_{\mathrm{L}}$, the logic zero voits supply, and the power zero volts $0 \mathrm{~V}_{\mathrm{P}}$, have been wired back separately to the power input area around IC3 to help ensure stability and an absence of noise problems with the logic supplies. GREAT CARE must be taken when wiring up the circuitry and assembling components on the Veroboard, and tests should be done prior to connecting to the computer as far as
possible. I can assure you, from practical experience, that connecting +12 V to the data lines by accident will certainly cause some interesting permanent changes to the way that your computer operates!
$\mathrm{V}_{\text {ref, }}$, and the half rail reference to IC7 pin 7, are both derived from the $+V_{P}$ rail to ensure tracking of the motor drive outputs if $\mathrm{V}_{\mathrm{P}}$ varies at all under different load conditions.

This circuit has successfully been used to control a 12 volt model train set by microcomputer. The only programming requirement is to output the relevant motor speed values to the port or ports in question. Hence, for a port address of 24 (Hex) for example, the assembled Z80 machine code for full speed forwards


Fig. 9. Veroboard layout
could look like this

3E Øの LD A, ØFFH
; Put required value in Accumulator.
D3 24 OUT ( 24 H ), A
; Output the Accumulator to the port.
In BASIC, the simple instruction OUT 36,

255 would suffice. ( 36 is the decimal equivalent of 24 H , the port address, and 255 the decimal equivalent of 0 FFH .) For full speed reverse use the value $\emptyset \emptyset \mathrm{H}$ ( $\varnothing$ decimal), for stopped use $\emptyset 7 \mathrm{FH}$ ( 127 decimal), and for slower speeds use values in between. Finally,
don't forget the heatsink on IC7! The i.c. has been placed at the edge of the board to allow for this. The resulting motor speed control provides a simple illustration of a typical use for power op-amps, either as two single devices or a pair as used specifically in Fig. 9.


## MAINS MONITOR PROJECT

## EyERYDAY ROMTCS <br> and computer PROJ=cTS

FEBRUARY 1985 ISSUE ON SALE FRIDAY, JANUARY 18

JOHN M. H. BECKER

ANY electronics enthusiast needs a signal generator and frequency meter nearly as much as a soldering iron and multimeter. The last two should be part of anyone's workshop but the degree of enthusiasm does not necessarily warrant the expense of highly accurate generators and côunters. Often only an indication of approximate frequencies is required, together with a unit that makes readily controllable sounds with suitably shaped waveforms.

## GENERATOR CHIP

An XR2206 function generator chip has been chosen in preferance to the normally selected type 8038 as it has a greater variety of waveforms available, together with a wider sweep range on each selected setting. The oscillograms show the wide range of waveforms available. The basic frequency range is selected by S 1, bringing in the desired frequency setting capacitor $\mathrm{C} 4-\mathrm{C} 7$. The frequency generated


This unit has been designed as a reasonable quality, moderate cost, dual purpose unit suitable for average and addicted constructors alike. It produces well shaped waveforms of frequencies ranging from 2 Hz to 78 kHz in-four tunable ranges, and includes automatic ramp control of a frequency sweep, both upwards and downwards. Additionally it includes a frequency to voltage converter that can be coupled to an ordinary multimeter, or digital voltmeter to give a direct read out of the approximate frequency being generated, or fed in from an external source. It is intended for use with an existing power supply or, for short periods with batteries, from 9 V up to 18 V dc. Provision has also been made to mount discrete power supply components directly onto the p.c.b. so that the unit can be fulfy independent of other equipment.
can then be controlled by either a varying voltage or a varying current. For normal manual selection of the desired frequency, current control is used, and is relative to the resistance of the total of VR4, VR5 and R8. In this mode VR5 is taken directly to ground by S5. As the resistance of these potentiometers decreases, so the output frequency rises in relation to the formula: $f=1 /(R \times(C / 1000)) \times$ 1000, where C is the value of the selected capacitor C4 to C 7 in microfarads, and R is the total resistance in circuit with pin 8 of IC2.

VR4 provides coarse tuning of the frequency, and VR5 fine tuning. The maximum resistance range that is permissible with $I C 2$ is from 1 K to 2 M , though is limited to a maxjmum of about 1 M in this unit. This allows a reasonable overlap between the switched ranges, without making the

Photograph illustrating the external assembly of the Signal Generator and-F-V Converter

## TEST GEAR PROJECT

## SPECIFICATION...

## TOLERANCE

The figures quoted refer to those obtained on the prototype and may vary slightly in other units in accordance with normal component tolerance factors.

## FREQUENCY TO VOLTAGE CONVERTER

Good linearity from 200 Hz to 30 kHz directly readable on a standard multimeter or digital voltmeter. Accessible internally and externally.

## FREQUENCY GENERATOR

Basic switched frequency ranges $=(1) 2 \mathrm{~Hz}$ to 81 Hz , (2) 20 Hz to 851 Hz , (3) 200 Hz to 8400 Hz , (4) 1970 Hz to 78800 Hz . Coarse and fine tuning of selected frequency range. Switch selected waveformssine, triangle, square, ramp, pulse, and variations (see photographs $1-6$ ). Sweep modulator-rising and falling ramps, switch selectable, rate 6 to 40 cycles per minute. Frequency outputs-switched, buffered or unbuffered via amplitude control from nil to 5 V peak to peak. Fixed $O V /+5 \mathrm{~V}$ amplitude square wave derived from internal oscillator or external source up to about 80 kHz . Four switched reference frequencies.


Fig. 2. Complete circuit diagram of the Signal Generator and Frequency-Voltage Converter
fine tuning too coarse. Switching in VR3 by S6 instead of VR4 and 5, a preset reference frequency can be selected. The i.c. contains its own current controlled amplifier and the amplitude of the signal generated as seen at pin 2, is presettable by VR6. This controls the sine, triangle, and ramp waveform maximum levels. The squarewave however is derived from a different section and is at approximately full line level amplitude as determined by the current through the load resistor R12. The shape of the triangle and ramp waveforms is predetermined within IC2 itself. For sine wave related waveforms, shaping is preset by VR8, and the symmetry trimmed by VR7.

## WAVEFORM SELECTION

Three basic waveform selections can be chosen with S2. With S8 open, the choice is sine, triangle and square. In position 1 (sinewave) the output comes from pin 2 of IC2, and VR8 is in circuit, controlling the sine shape. In position 2 , (triangle wave), the output again is from pin 2, but at a level approximately twice that of the sine wave and VR8 is out of circuit. In position three (squarewave), the output is taken from pin 11 IC2. With S8 closed the squarewave is directly fed to the control pin 9, and internal circuitry of the chip is automatically switched by it to produce ramp related waveforms in the first two positions of S2. In this mode the frequency of oscillation now becomes affected by the value of R9 and the formula changes to: $f=(2 / C / 1000) \times(1 / R) \times$ 1000, using the same parameters as before. Effectively this means that the frequency with S 8 closed will be approximately twice that with it open. In position S2, looking at the inverted output of IC1C, the rising ramp is sine shaped, followed by the steep drop. In position 2 the rising ramp is linear, again followed by a steep drop. Study of the second formula though will show that the steepness of the drop is related to values of R9, and the controlling resistance on pin 8. As the two resistances approach equality, so the steepness lessens, and a falling ramp also develops. The best ramps are thus created with the resistance on pin 8 at the greater end of the scale. In position 3 the output is again from pin 11, but consists of a mark-space pulse, the duty cycle of which determined by the formula: $R A /(R A+R B)$, where RA is the resistance on pin 7, and RB that on pin 8 . The negative going pulse length is moderately constant throughout the range for the same capacitance selection. The mark-space factor is also reflected in the shape of the ramps with a flattening of the apex, but is really only noticeable at small values of capacitance.

## OUTPUT ROUTING

In most instances it is preferable for the amplitude of the different waveforms seen at the final output to be roughly equal. As previously seen there is an inherent level difference between the three main waveform ranges, IC1C is thus included to even these out. The gain of this stage is of course dependent upon the relationship of the total input resistance to the value of the feedback resistor R16. The choice of resistors R13-R15 ensures a reasonable match of the levels. The inverted phase output from IC1C is decoupled by C9, taken via S3 to the level control VR9 and then to the output via S9. However the frequency pass range of IC1C is less than that of the range available from IC2. For normal audio applications, the frequency response of IC1C is sufficiently adequate, but distortion becomes more prevalent as the frequency rises above about 30 kHz , as shown in the oscillograms.

Additionally the loading of C9 causes square wave distortion at lower frequencies. S3 is thus included to bypass IC 1C so that the output is unbuffered allowing the full range of IC2 to be used. Note though that the unbuffered output also contains a d.c. bias that is approximately half line level with S2 in positions $1 \& 2$, and that the phase is inverted.

## SWEEP OSCILLATOR

When testing out some circuits it is sometimes preferable for the frequency range to be swept upward or downwards at a controlled automatic rate rather than by manual control of a potentiometer. The ramp generating circuit around IC1A \& IC1B provides this control. The frequency range of ramp generation is determined by C1 with larger values giving slower rates. VR1 provides the tuning of the sweep rate setting. The direction of the ramp produced is governed by the direction of voltage flow through D1 and D2. S4 selects the diode routing, and reverses the polarity of the controlling voltage through VR1 in relation to the reference level at C2. The changing d.c. voltage produced by the ramp controls IC2 via VR2, S9, VR4 and VR5. In this mode voltage control of IC2 is being employed in additior to current control. For correct operation of IC2 the voltage sweep seen at the wiper of VR2 must lie below 3 V , above this and the oscillator of IC2 will cease. VR2 thus needs adjustment to keep the sweep voltage within this range. The frequency control range provided by the varying voltage is less than that produced in the manual mode, and VR4 and VR5 are used to select the desired band width.


Sine (normal) S2,


Sine (ramp) S2 $\mathbf{1}_{1}$


Triangle (normal) S2 $\mathbf{2}_{2}$


Triangle (ramp) $\mathbf{S 2}_{\mathbf{2}}$


Square (normal) \$23


Square (pulse) $\mathbf{S 2}_{3}$


Sine (high freq) $\$ 2{ }_{1}$


Triangle (high freq) $\mathbf{S 2}_{2}$


Ramp (high freq) $\mathbf{S 2}_{3}$

## FREQUENCY TO VOLTAGE CONVERTER

IC3 performs the f-to-v conversion, producing an output voltage that, within the range, is related linearly to the frequency fed in. The range available is determined by the gain given to the feedback via R27 and VR11, with a slew rate and ripple reduction level set by C14. High values for C14 will give reduced ripple for lower frequency signals, but will increase the time taken for the voltage to stabilise when the frequency is changed. The relative minimum output voltage in the absence of an input frequency should be as close to zero as can be set by the bias control VR10. VR11 is used to set the maximum range. The output voltage is referenced to an intermediate level of about 5 V as set by Zener diode D5. The negative lead of the meter used to monitor the voltage is taken to this level, and the positive lead to the output from pin 12, IC3. If the meter negative lead were to be taken to the normal OV or ground line then the reading would also contain the reference voltage of 5 V and inaccurate readings would result. For stable operation of the conversion, the input frequency seen at pin 11, IC3 should be at a constant level of about iV p-p. To maintain this amplitude even for low level input signals, the signals are taken via the gain stage IC1D for external signals which gives an amplification of about, a little over 100. The signal is then attenuated to the optimum level by diodes D3 \& D4. For internal frequency reading, the signal is taken direct from the output of IC1C, and similarly attenuated. S7 selects the choice of internal or external frequency monitoring. In addition to producing a frequency related voltage, IC3 also produces a square wave output of 5 V amplitude. There is a slight time lag between the edges of the input frequency and of the out-
put 5 V squarewave. S 9 can switch in this frequency output in place of that produced directly by IC2. This means that an external frequency of indifferent level and shape can be converted for controlling circuits that require a 5 volt squarewave. The external loading permissible though is limited by the value of R30 and too great a load will reduce the voltage.

## POWER SUPPLY

Most enthusiasts probably already have power supplies in their workshop capable of driving this unit, and so a separate one is not included. The minimum voltage requirement is 9 V , and the maximum permissible +18 V as dictated by the limits of IC3. The current drawn is about 30 mA , up to 20 mA of which is consumed by IC2. This current is a bit too high for the unit to be powered for long periods from a battery supply, though one could be used briefly in an emergency. Alternatively a battery eliminator might be suitable, providing it can tolerate the current without the voltage dropping below 9 V and that the ripple content is negligible. The printed circuit board though includes positions for the mounting of the rectifier and voltage regulator as shown in the suggested optional 12 V power supply circuit. This supply was not used in the prototype and is not regarded as an integral part of the project. The transformer should be bolted to the metal box, and normal mains electricity safety precautions observed. Note that with this suggested power supply C18 has its positive end connected to a different track position, and it may be necessary to mount it vertically rather than horizontally. The use of a heat sink with the regulator i.c. should not be necessařy.

## COMPONENTS

## RESISTORS

R1,R7,R15,R17,R22. R25-R27
R2,R3,R18,R19
R4
R5
R6
R8,R10,R11,R12,R21
R28-R30
R9, R24, R31
R13
R14
R16
R20
R23
All resistors $\frac{1}{6} W \pm 5 \%$
CAPACITORS
C1-C3,C8-C10,C17 C4
C5,C11,C12,C14-C16, C19,C20
C6
C7

C13
C18

## SEMICONDUCTORS

IC1

## IC2

IC3
D1-D4
D5

56 p polystyrene
$470 \mu, 25 \mathrm{~V}$ elect.


## MISCELLANEOUS

P.c.b. and p.c.b. clips (4 off)

Round knobs ( 6 off)
I.c. sockets, 16 pin, 14 pin (2 off)

Jack socket, 3.5 mm
Jack sockets mono (2 off)
Box and rubber feet
Meter terminals (2 off)

## SWITCHES

| S1,S2 | 3P4W (2 off) |
| :--- | :--- |
| S3,S5,S7-S9 | SPDT (5 off) |
| S4,S6 | DPDT (2 off) |

## Constructor's Note

A complete kit of parts is available from: Phonosonics, 8 Finucane Drive, Orpington, Kent BR5 4ED. Price $£ 54.00$, inclusive of VAT. Post and packing £1.00.

## ASsEMELY

After the straight forward component assembly and subsequent joint checking procedure has been carried out, wiring should be commenced in a methodical fashion, ticking off each wire on the wiring diagram as connections are made. First connect up all the panel controls between themselves. Secondly wire up to all the p.c.b. points closest to the front panel. Finally connect up the rear and remaining connection points. These latter wires should preferably be brought under or round the edges of the p.c.b. Taking them over makes the wiring untidy. Keep the wiring short, but long enough for turning the board over for examination without over straining the connections (too much flexing of taut wires can cause breaking at the joins). The prototype has the meter terminals on the front, but with hindsight, mounting them on the back would be better.

The regulator IC4, and the rectifier REC1, are part of the optional power supply, together with the transformer T1. These components may be omitted if not required as the unit will run quite efficiently from any 9 V battery.

## SETTING UP

A fair selection of presets has been included to enable the maximum accuracy to be obtained throughout the unit. The only really critical one is VR2, as the sweep control may not operate if this is incorrectly set. Inadequate setting of the others will only cause lack of linearity. If an osćilloscope is not available intelligent decisions will need to be made, listening to the sounds while adjusting the presets.

First, S1 position 1 (lowest freq), S2 position 1 (sine), S3 on (buffered output), S4 either way, S5 off (sweep off), S6 off (manual freq control), S7 off (internal f-v), S8 off (standard waveforms), S9 off (vco output), VR1-3 midway, VR4-5 max clockwise (highest freq), VR6-8 midway, VR9 max, VR10-11 midway. Switch on and check that pin 3 IC1A, pin 3 IC2 are at approximately half line voltage, and that the positive end of D5 is at about 5 V . Plug in to normal amplifier. If no sound is heard then check the wiring, and that the switches are wired the correct way up. Assuming that sound is heard, check that VR4 and 5 vary the frequency, and that S1 changes the ranges. Switch on S6, and adjust VR3 to the desired fixed frequency on the second range of S1. In the author's unit this was set for approximately 440 Hz . Check that S 8 brings in the ramp associated


Fig. 3. (Above) Showing the p.c.b. design and component layout of the Signal Generator. (Left) Photograph illustrating the internal view of the chassis assembly showing the switch, sockets and p.c.b. layout


Fig. 4. Wiring diagram of the Signal Generator
ranges of waveforms, then switch back to the normal range, and to squarewave. Monitor the output jack socket and note the squarewave amplitude level. Switch to triangle wave and adjust VR6 untif the amplitude is similar without flattening of the waveform peaks. Switch to sine wave and adjust VR8 for the best sine shape, then VR7 for the best symmetry. If necessary readjust VR8

Switch S3 to bypass and check all waveforms can be switched in, though as previously stated they will be at widely varying levels. Switch S6 back to manual control, then S5 to sweep control. Check that a ramp waveform appears at pin 1 IC1A, and that switching 54 varies the direction, also that VR1 varies the rate with the ramp in both directions. Return scope probe to the output jack socket, and adjust VR2 for the smoothest sweep response. If the wiper is too far to the OV end the generator frequency will dwell at the high end, with it too far towards IC1 the generator will cut out at the low frequency end. With careful adjustment a smoothly varying rising or falling sweep range can be set. Switch off the sweep control and set a frequency output from IC2 of precisely 10 kHz . Check that an attenuated version of this frequency reaches pin 11 IC3 via S7. With the external input jack socket grounded (as it will be without a jack plug in), switch S 7 to external. Connect a multimeter across the meter output terminals and adjust VR10 for a reading of exactly zero volts. Start off with a meter range of
about 5 volts, then after the initial adjustment has been made the meter can be switched to its lowest range for greater precision. Set meter to a range for monitoring exactly 1 V . Switch S 7 back so that the 10 kHz signal reaches IC3. Very carefully adjust VR11 until a precise voltage of 1 volt is obtained.

The maximum frequency that can be read will be about 30 kHz to 35 kHz , beyond this IC3 will fail to respond and show a constant reading of around 3.5 V . Applying a 1 kHz signal should produce approximately 0.1 V . Tracking downwards in frequency, linearity will be roughly maintained until about 200 Hz or so, depending on the accuracy of the setting of VR10 and VR11. Once the boundary extremes have been established, a direct reading of frequency can be taken from the multimeter by converting the voltage into the readily calculable frequency. Thus if $1 \mathrm{~V}=10 \mathrm{kHz}, 3 \mathrm{~V}=$ $30 \mathrm{kHz}, 0.5 \mathrm{~V}=5 \mathrm{kHz}, 0.05 \mathrm{~V}=500 \mathrm{~Hz}$, etc. Check that an external frequency can be monitored in the same way, then finally that a squarewave output of about 5 V is available from pin 8 to IC2

After setting up the $f-v$ converter the frequency controls of the unit can be calibrated and control legends applied to the panel, using a rub down lettering like letraset or similar, then coating them with a suitable spray protector. If care has been taken in the setting up, the end result will be a marvellously versatile dual purpose new unit for the workshop. $\star$


## RING MASTER

Perhaps the most interesting development during the past few months has been the visual detection of the ring-system surrounding Uranus. The rings were first found indirectly, because they produced a series of occultations of a faint star; subsequently, D. A. Allen and J. Crawford, at Siding Spring Observatory in Australia, photographed them in infra-red.

Studies of them have now been carried out by Richard Terrile and Bradford Smith, using the $2 \cdot 5$-metre reflector at the Las Campanas Observatory in Chile together with a highly sensitive CCD or Charge-Coupled Device. The ring-system is clearly shown, together with all five known satellites-Miranda, Ariel, Uimbriel, Titania and Oberon. The pictures show the great power of the CCD, which is at least thirty times more sensitive than any photographic plate.

The rings of Uranus are quite unlike those of Saturn. Terrile and Smith find that their albedo or reflecting power is only about 2 per cent, so that they are blacker than coal-dust. They are also narrow; there are at least eight
rings, not all of which are perfectly circular, and their composition is unknown.

If all goes well, we should learn more about them in January 1986, when the Voyager 2 spacecraft makes its pass of Uranus, Meanwhile, there is speculation about the possibility of a ring-system round the outermost giant, Neptune, but the presence there of a large retrograde satellite (Triton) may have prevented any rings from being formed. Again, we pin our hopes on Voyager 2, which will rendezvous with Neptune in the late summer of 1989.

## HALLEY'S COMET

Halley's Comet is, of course, still much too faint to be detected except with very powerful instruments, but recent studies show that it may prove to be somewhat brighter than had been expected. Unfortunately, this does not mean that it will be a brilliant spectacle, as it has been on many past returns.

It should become a naked-eye object at the end of 1985 , before perihelion passage on 9 February, 1986, but British observers will need clear skies. When at its best, after perihelion, the comet will be in the far southwell placed for Australians and South Africans, but not for Europeans, who will not see it at all until it has faded considerably.

## NOVA CYGNI-A NEW LOOK

On the evening of 29 August, 1975, I went into my observatory to make some routine observations of variable stars. When I looked up at the familiar constellation of Cygnus, I had a surprise. There, shining down unmistakably, was a bright star which had certainly not been there on the previous night. I estimated its magnitude as 2.4 , slightly fainter than Gamma Cygni, the central star of the "cross" of Cygnus.

Having satisfied myself that it really was a new star or nova, I made a telephone call to the observatory at Herstmonceux. I was, of course, fairly sure that the star had already been reported-and so it proved; it had been discovered some hours earlier by Kentaro Osada in Japan, before darkness fell over England. I imagine that I was äbout sixtieth in the list of independent discoverers; the star could not possibly have been overlooked by anyone with more than a rudimentary knowledge of the constellations.

The most remarkable fact about Nova Cygni was that it brightened up by at least nineteen magnitudes in only a'few hours. This was a record, both for amplitude and for speed. Its decline was also unusually quick. I estimated its magnitude as 1.8 on 30 August, so that it was then much the brightest star in the constellation apart from Deneb; but it had dropped to below 3 by 1 September, below 5 by 4 September, and faded below naked-eye visibility by 7 September, when I saw it as fiery red-in fact, as red as any star I have ever seen. Within a few months it had become too faint to be observed except with powerful telescopes.

Apart from Nova Cygni, only three novae seen since 1930 have attained the first magnitude: DQ Herculis (1934), CP Lacertae (1936) and CP Puppis (1942), though others have become visible with the naked eyenotably HR Delphini, which was discovered in 1967 by the well-known English amateur George Alcock and had a very prolonged maximum of around the fourth magnitude. It is still above magnitude 13 , and probably will not fade much further, as this was also its preoutburst magnitude.

However, the exceptional behaviour of Nova Cygni has led to particularly detailed studies of it, and efforts have been made to detect a cloud of débris round it. This has now been a successful operation.

## THE SKY THIS MONTH

Winter skies are always glorious, thanks to the presence of Orion, the Hunter, and his magnificent retinue, but at the moment the dearth of bright planets continues-apart from Venus, which is at its very best in the evenings. Mercury is, in theory, a morning object, and may indeed be glimpsed just before sunrise, but it is well south of the celestial equator, so that European observers are unfavourably placed.

Mars may be seen in the south-west during the early evening, and moves from A quarius into Pisces by the end of the month, but its magnitude is now onlv 1-2, and no telescope will show much upon its surface. Saturn, in Libra, rises well before the Sun, but is low down and by no means prominent, while Jupiter passes through conjunction on 14 January and is therefore out of view altogether. There are no eclipses this month, and no bright comets are expected. The Moon is full on 7 January, and new on the 21 st.

During winter evenings the brilliant yellow star Capella is almost overhead (a position occupied by the equally brilliant Vega during evenings in summer). Close beside Capella lie the three fainter stars making up a triangle. They have been nicknamed the Haedi or 'Kids', and two of them are very remarkable objects.

Epsilon Aurigae, at the apex of the triangle, is an extremely luminous supergiant, at least 60,000 times as powerful as the Sun. Every 27 years it fades down by almost a magnitude, not because it is intrinsically variable but because it is being eclipsed by a companion which has never been seen at all.

The nature of the invisible secondary is still a matter for debate. It was once believed to be a very young star, not vet hot enough to shine; there were also suggestions that it might be a black hole, but it now seems more likely that it is a relatively small, hot star with an associated extensive shell of material. The last eclipse ended in 1984, so that for more than two decades nothing further will be happening.

Look at the 'Kids' and you will see that Epsilon is now the brightest member of the trio. The faintest, Sadatoni or Zeta Aurigae, is also an eclipsing binary with a period of 972 days, but we know much more about it; the primary is a red supergiant, while the secondary is a much smaller and hotter star.

It is sheer coincidence that these two exceptional eclipsing binaries lie side by side in the sky. There is no true connection between them; Epsilon is much further away from us than Zeta.

Using the 82 -inch reflector at the McDonald observatory in Texas, G. and A. de Vaucouleurs have recorded the debris unmistakably. The cloud shows up as an elliptical blur, $3.5 \times 2.5$ seconds of arc across, with an integrated magnitude of about $16 \frac{1}{2}$. Presumably it is expanding; and if the distance of the nova is 4,500 light-years, as seems likely, the expansion rate is approximately 800 miles per second.

## BINARY SYSTEM

According to modern theory, a nova is a binary system, made up of an ordinary main sequence star together with a white dwarf. White dwarfs are stars far advanced in their evolution; they have used up their nuclear "fuel", and have become very small and almost incredibly dense.

In a nova, the white dwarf pulls material away from its larger, less dense companion, and there is a build-up of material around the dwarf, leading eventually to instability and a violent, usually short-lived outburst. Associated débris is only to be expected, and has been detected with many former novaesuch as Nova Persei 1901 and Nova Aquilae

1918, both of which became much more brilliant than Nova Cygni. Indeed, for a brief period Nova Aquilae outshone every star in the sky with the exception of Sirius.

## SUPERNOVAE

There is a fundamental difference between ordinary novae and the much more powerful supernovae, which are much less common. Only four supernovae have been seen in our Galaxy during the past thousand years; those of $1006,1054,1572$ and 1604 -all before the invention of the telescope, though supernovae are so luminous that they may be detected in external galaxies many millions of light-years away.

From the few accounts which have come down to us, the 1006 supernovae, in the southern constellation of Lupus, became as bright as the quarter-moon, while the other three outshone Venus. The 1054 supernova has left the gas-cloud of the Crab Nebula, which contains a pulsar.

For many years the Crab was regarded as unique, but recently a very similar supernova remnant, including a pulsar, has been. found in the Large Cloud of Magellan, more than

150,000 light-years from us. Pulsars are rapidly-spinning neutron stars which slow down as they age. From the measured slowing-down of the Large Cloud pulsar, it has been estimated that the outburst occurred about a thousand years before our present-day view of it.

The rapid increase of Nova Cygni 1975 raised initial hopes that it might be a supernova-something which astronomers would warmly welcome, because it cannot be said that our knowledge of supernova mechanism is at all reliable (there seem, indeed, to be two quite different types of supernovae, one of which involves the collapse of a massive star while the other indicates the complete destruction of a white dwarf).

We could learn much more if we had the opportunity to study a relatively nearby supernova with modern equipment. Nova Cygni was therefore something of a disappointment; but it is still extremely interesting, and it will be important to find out how the newlydiscovered cloud of débris develops.

There is one rather sobering thought. When we look out into the Galaxy, we are also looking into the past. Nova Cygni exploded well over four thousand years ago; the expanding cloud we see today was produced long before astronomy had become a true science!

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## THERMISTOR

## THERMOMETER



CALIERATION OF METER 1 mA FS. 0
Construction and calibration of the Thermistor Thermometer

| ${ }^{\circ} \mathrm{C}$. AT | 0 | 30 | 70 | 100 |
| :---: | :---: | :---: | :---: | :---: |
|  | +3.3 | -2.0 | + 1.7 | -2.6 |
|  | +4.0 | -2.5 | +2.2 | -3. 2 |
| TABLE | + |  |  |  |

THE conventional bridge circuit recommended for thermistors is somewhat inaccurate. Better results can be obtained using the arrangement shown here. The op.amp, IC2 acts as a voltage source, with current measured by the meter ME1. This configuration corrects for most of the thermistor's non-linearity. An offset current flows through R5 and VR 1, and sensitivity is set by VR2 and R6. Assuming a fullscale current of 1 mA , an output of $1 \mathrm{mV} /{ }^{\circ} \mathrm{C}$ is conveniently obtained at the output and this can be used to drive a chart recorder, for example. The supply voltage is regulated by IC 1 , and a 3 -way switch allows the battery to be checked. Resistor values for two types of NTC thermistor are given in Table 1. JA-03 is metal-sheathed (RS no. 151-120) and VA3704 (Mullard no. 2322-62711472) is a glass-bead device. Both have a resistance at $50^{\circ} \mathrm{C}$, of the order of 1 k 7 .

Kettles and ice-buckets are unpredictable gadgets! Calibration was done at 10 , 50 and $90^{\circ} \mathrm{C}$, using a water-bath and laboratory-grade mercury thermometer. The error curve is cubic, with a deviation within 2 or 3 degrees centigrade over most of the range, increasing near the $0^{\circ}$ and $100^{\circ} \mathrm{C}$ limits.
C. J. D. Catto,

Elsworth,
Cambridge.


PEIOM

## LOGIC RECORDER

THE logic recorder is designed to fill the gap between the logic probe and the logic analyser by displaying a sequence of eight data bits on a bank of l.e.d.s. Data is stored synchronously with the system clock after a trigger pulse from the circuit under test.

Data is fed into 1C4, an octal D-type flip-flop wired as a shift register, though a 74LSI 64 shift register could be used instead. D2 represents the most recent data.

Suppose that latch $1 \mathrm{Cl} 1 \mathrm{a} / \mathrm{b}$ is set so that D10 is unlit. IC1 pin 6 is high so IC3 is reset, its ' $A$ ' output is low, IC Id is disabled and IC1C is enabled via IC2b. When the ARM button is pressed the latch sets, lighting DIO and freeing IC3 to count. On the rising edge of IC 2 c pin 8 , the single-bit counter in IC3 clocks, disabling IC1c and the ARM button and enabling ICId to clock IC4 and, via IC2d, the 3-bit section of IC3.

After eight clock pulses from the system under test, IC3 pin 11 goes low, resetting the latch via C1. Provided that the ARM button has been released the logic recorder resets and displays the data received until it is rearmed.

IC2a and IC2c are used as programmable inverters to select the desired trigger and clock edges. DI protects the recorder against reverse polarity on its power supply leads which are connected to the test circuit.
G. Strange,

Loughborough, Leics.


May be I or 0
D7 D6 D5 D4 D3 D2 D1 D0 $\begin{array}{cccccccc}\text { I } & \text { I } & \text { X } & \text { X } & \text { X } & \text { X } & \text { X } & \text { X } \\ 128 & 64 & 32 & 16 & 8 & 4 & 2 & 1\end{array}$ $\begin{array}{llllllll}1 & 1 & 1 & 0 & 1 & 0 & 1 & 1\end{array}$
e.g. D2 and D4 are low
$128+64+32+0+8+0+2+7=235$

Table 1. Showing example of IN127 command

A. Moran

Reading,
Berks.

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DIN LEAD

TESTER

$H$-AVE you ever wondered whether all your problems might just be due to a faulty DIN lead? If so, you'll no doubt have discovered what an awkward operation it can be to test one; but here is a simple solution.

The following design will test DIN leads for open circuit, short circuit and wrong connections all in one go. Whereas with a continuity tester you need to test each pin individually, this circuit gives an immediate indication of the connections (or lack of connections) between pins at either end.

IC1 is a 4017, which is a decade counter with decoded outputs. It sends each pin high, in sequence, moving on to the next
one every time it receives a clock pulse. For a 5 pin DIN, the sixth output is connected to reset and thus counts through $0,1,2,3,4$ and 5 . Six pulses are allowed to enable the screen to the tested separately (note however that this is often connected to the middle pin). The clock used to drive ICI is produced by a standard CMOS oscillator based around IC2 (a 4011 quad NAND), the NAND inputs being shorted together as shown to act as inverters. This i.c. type was chosen merely so that fewer gates were left unused. A hex inverter would serve just as well. IC3 and IC4 are 4050 hex buffers used to drive the l.e.d.s.
The clock frequency is normally about 1 kHz , providing an apparently constant display. In this mode any broken connections will immediately show up as unlit l.e.d.s. at ' $B$ '. By pressing switch S1 the 68 k resistor R 1 , is disconnected and the clock frequency reduced so that a more detailed representation of the condition of the DIN lead is given. Two common types of 5 pin DIN lead exist; straight through and mirror image.
STRAIGHT THROUGH-L.e.d.s at 'A' and ' $B$ ' should light in the same order.
MIRROR IMAGE-L.e.d.s at ' $A$ ' and ' $B$ ' should light in opposite orders. Crossed leads can thus be detected by incorrect orders at ' $B$ '

Any two l.e.d.s lit simultaneously at one end in this mode indicate shorted leads at that end.

Some sample displays are given. Using CMOS logic, the unit can be readily powered by a 9 V (PP3) battery.
C. Walden,

Selby,
S. Yorks.
(Above) Some possible fault indications
(Below) Complete circuit diagram of the DIN Load Tester


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[^2]
## CONSTRUCTION

Construction starts with axis 0 and progresses upwards from there. The hydraulic cylinders of the NEPTUNE are supplied pre-assembled. First axis 0 cylinder is fitted to its sensor potentiometer, on a bracket beneath it , and then to the base plate and front plate (Fig. 6:1). There are support brackets to ensure a rigid structure and there are triangular brackets with feet on them to prevent the robot from tipping over when under load. The top slot in the rear plate is for fitting the computer interface leads to the edge connectors on the interface board. The slot beneath it is for the cables leading to the power supply which fit onto the rear plate later.

Next the top plate is fitted. Being 3 mm steel this is quite heavy but this is necessary to ensure rigidity. On top of axis 0 cylinder goes the shoulder rotating axle with axis 1 mounting plate on top of it (Fig. 6.2). The weight of the arm is carried by a large thrust ball race fitted round the axle. Through the axle passes the plumbing/wiring harness which is secured to axis - 1 cylinder fitted to the mounting plate.

Onto mounting rings on axis 1 cylinder the lower arms are fitted and to the upper end of these are fitted axis 2 cylinder with the upper arms attached to it (Fig. 6.3). To the end of the upper arms is fitted axis 3 cylinder which provides the wrist raising function.

A pair of mounting plates is used to secure axis 4 cylinder to the front end of axis 3 cylinder (Fig. 6.4). This applies to NEPTUNE II only, where it provides wrist yaw, a function immensely useful when picking up objects lying flat or in other difficult positions. It also greatly assists spraying into corners. Yaw is a feature usually found on only the most expensive of robots used in industry. Axis 5 , the wrist rotation cylinder fits to the axle of axis 4 cylinder by means of a short plate. On NEPTUNE I where there is no wrist yaw, axis 5 fits to the top of axis 3 cylinder. The gripper clamps onto the axle of axis 5 cylinder with a single set screw enabling it to be rapidly changed. The NEPTUNES are supplied with a choice of gripper types. The robot is now ready for plumbling and wiring.


Fig. 6.1. (above): base plate and axis 0 cylinder
Fig. 6.2. (opposite): shoulder-rotating axle with axis 1 cylinder fitted to the mounting plate


## ROBOTICS PROJECT

The harness is strapped onto the arms at the fixing holes with cable ties. The position for these is marked, with dabs of paint, on the harness. The pipes press into 'banjo' fittings attached to the cylinder ends with Delrin hollow bolts and the cables are trimmed and soldered to the sensor potentiometers (Fig. 6.5).

The solenoid operated valves, which control the water flow, fit with hollow bolts to a Delrin manifold (Fig. 6.6) which acts like a printed circuit board routing the water to the correct valve. The other end of the valves fit to bored Delrin bars to which the restrictors and flow rate control valves also fit (Fig. 6.7). Brackets to which the solenoid driver boards will fit are screwed to the solenoids and ensure correct alignment for the boards which clip onto the connector tags of the solenoids (Fig. 6.8). This arrangement avoids soldering to the solenoids and greatly simplifies maintenance in that the boards can be rapidly unplugged from the system. Connections to the plumbing harnes's
again are made with "banjo" push-on fittings and hollow bolts.
After wiring up the power supply (Fig. 6.9) and connecting to the computer interface board (no need to connect to a computer yet) the system is ready for commissioning. The sump of the hydraulic power pack is filled with water and the pump is operated with its outlet and inlet connected together with one of the plug-in pipes. This expels the air from the pipe which, after switching off the pump, is plugged into the manifold as the pressure source; the return pipe is taken from the outlet of the manifold to the sump. After pressurising the system and checking that there are no leaks the axes are tested one at a time by plugging in a solenoid driver board and the axis operated by means of a potentiometer on CN401 extend-contract connector. This will drive out most of the air. The rest of it will gradually disappear by dissolving in the water when under pressure. It then comes out of solution when returned to the sump.


Hydraulic cylinder assembly


Fig. 6.4. Shoulder, upper arm and wrist assembly


Fig. 6.5, Plumbing and wiring loom


Fig. 6.6. Hydraulic control manifold


Fig. 6.7. Assembly showing restrictors and flow-rate control valves


Fig. 6.8. Completed hydraulic flow-control sub-system for all seven axes

All the solenoid driver boards may now be fitted (Fig. 6.10), the computer interface board connected to the computer and the "NEPDYN" program run. This sends and returns the chosen axis between 2 points and generates, on the monitor screen, a graph of error in the axis position against time. The error is the difference between where the axis is, as measured by the ADC, and where the axis has been told to go. With the aid of this program the restrictors are set to achieve rapid convergence of the send and return graphs without any overshooting.

After setting the restrictors of each axis, the pre-sets on the solenoid driver boards are set so that sending position 0 from the computer, by means of the "NEPTROL" program, sends each axis to just before the end of its travel. The pre-sets on the interface board are set to match the positions of the simulator (Fig. 6.11 ) with the positions of the robot.

The interface board is next mounted over the manifold assembly (Fig. 6.12) which is then slid into the robot base and bolted down. Following fitting of side plates and covers the robot is then ready for use.

## OPERATION OF THE ROBOT

Operating the robot basically consists of using POKE and PEEK instructions sent to the robot as if it were part of the memory of the computer. To move axis 0 of the NEPTUNE II


Fig. 6.10. All sub-assemblies completed and wired up for


Fig. 6.11. NEPTUNE simulator arm
to position DO, the start of the 'memory' is first defined. This is also the address for the most significant byte of axis 0 . The least significant byte is at the next address. On the BBC, POKE and PEEK are represented by '?' and hexadecimal numbers are indicated by ' $\&$ '.

$$
\begin{aligned}
& 10 \mathrm{~A}=\& \text { FCOO } \\
& 20 \text { ?A=DO DIV } 16 \\
& 30 \text { ? (A + } 16=(\text { DO MOD } 16)^{*} 16
\end{aligned}
$$

The data DO can be any integer from 0 to $4095\left(2^{12}-1\right)$ because it is a 12 -bit control system. On the NEPTUNE I it is an 8 -bit system so the range is 0 to $255\left(2^{8}-1\right)$ so only one byte is sent for each axis move. For the msb the data is divided by 16 and the remainder ignored. For the lsb this remainder is multiplied by 16 because it is the top 4 bits of the Isb that are used.

The addresses of the axes follow successively so to move axis 4 to position D4 the instructions are as below.

$$
\begin{aligned}
& 40 ?(\mathrm{~A}+8)=\text { D4 DIV } 16 \\
& 50 ?(\mathrm{~A}+9)=(\mathrm{D} 4 \text { MOD } 16)^{*} 16
\end{aligned}
$$

Similarly for axis 5

$$
\begin{aligned}
& 60 ?(\mathrm{~A}+10)=\text { D5 DIV } 16 \\
& 70 ?(\mathrm{~A}+11)=(\mathrm{D} 5 \text { MOD } 16)^{*} 16
\end{aligned}
$$

The servo system of the robot then makes the axis go to this position with no further computer intervention but with the ADC the position of the axis can be followed as it is moving. To operate the ADC it is written to at $\mathrm{A}+14$. Data bit 7 is toggled and the multiplexer axis address set up. The axis address is in the bottom 4 data lines (see Table 1 October 1984). Axis 0 is at address 0000 . The msb is read at $\mathrm{A}+17$ and the 1 sb at $\mathrm{A}+16$.

$$
\begin{aligned}
& 80 ?(\mathrm{~A}+14)=128 \\
& 90 ?(\mathrm{~A}+14)=0 \\
& 100 ?(\mathrm{~A}+14)=128 \\
& 110 \mathrm{DAO}=?(\mathrm{~A}+17)^{*} 16+?(\mathrm{~A}+16) / 16
\end{aligned}
$$

Fig. 6.12. Control and servo


Similarly for àxis 4
$120 ?(\mathrm{~A}+14)=132$
$130 ?(\mathrm{~A}+14)=4$
$140 ?(\mathrm{~A}+14)=132$
150 DA $4=?(\mathrm{~A}+17)^{*} 16+?(\mathrm{~A}+16) / 16$

Reading the simulator is performed similarly but at the multiplexer axis address 8 bits higher so to read simulator axis 0 :

$$
\begin{aligned}
& 160 ?(\mathrm{~A}+14)=136 \\
& 170 ?(\mathrm{~A}+14)=8 \\
& 180 ?(\mathrm{~A}+14)=136 \\
& 190 \text { DSO }=?(\mathrm{~A}+17)^{*} 16+?(\mathrm{~A}+16) / 16
\end{aligned}
$$

If the simulator is constantly read and the data returned to the robot then the robot will follow the movement of the simulator.

NEXT MONTH: details of the assembly and use of MENTOR.

The complete NEPTUNE 2 robot system, showing the pump, computer and monitor, and the simulator



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# Sequential Logic Techniques Part 5 

## M.TOOLEY BA and D.WHITFIELD MA MSc CEng MIEE

AST month we carried out a detailed investigation of the operation of a universal shift register. This month we shall turn our attention to another device which finds a wide range of applications in the digital world, the data multiplexer.

Data multiplexers, or data selectors as they are sometimes known, generally have one output and several inputs. Any one of the inputs can, by placing appropriate logic levels on its control inputs, be routed to its output, Data multiplexers thus provide us with a means of sending several different digital signals along a common signal line.

In essence the data multiplexer acts as a multi-way switch however, by virtue of its internal logic and unlike its conventional analogue counterpart, the device will only operate with digital signals.

The switch equivalent of the simplest form of data multiplexer is shown in Fig. 5.1. This two-way arrangement


Fig. 5.1. Simplified switch equivalent of a two-way data multiplexer
is equivalent to a single-pole double throw (SPDT) logic switch. The two switch states are controlled by means of a third select input. When a logic 0 appears on the SELECT input the switch moves to position $A$ whereas, when a logic 1 appears on the SELECT input the switch moves to position B.

The internal logic of the two-way data multiplexer is shown in Fig. 5.2


Fig. 5.2. Logic arrangement of a twoway data multiplexer

This simply consists of two two-input AND gates, a two-input OR gate and an inverter. The truth table for this arrangement is given in Table 5.1. As

| $\mathbf{A}$ | $\mathbf{B}$ | $\mathbf{S}$ | $\mathbf{Y}$ |
| :--- | :--- | :--- | :--- |
| 0 | 0 | 0 | 0 |
| 0 | 0 | 1 | 0 |
| 0 | 1 | 0 | 0 |
| 0 | 1 | 1 | 1 |
| 1 | 0 | 0 | 1 |
| 1 | 0 | 1 | 0 |
| 1 | 1 | 0 | 1 |
| 1 | 1 | 1 | 1 |

Table 5.1. Truth table for simple twoway data multiplexer
can be seen, whenever the SELECT input is at logic $O$ the output, $Y$, takes the state of the $A$ input wheras, when the SELECT input is at logic 1, the output takes the state of the B input.

By grouping together the states for which the output remains unaffected by one or other of the inputs (we shall, for obvious reasons, call these the "don't care" states!), the truth table of the two-way multiplexer can be reduced to that shown in Table 5.2.

| $\mathbf{A}$ | $\mathbf{B}$ | $\mathbf{S}$ | $\mathbf{Y}$ |
| :---: | :---: | :---: | :---: |
| 0 | $\times$ | 0 | 0 |
| 1 | $\times$ | 0 | 1 |
| $\times$ | 0 | 1 | 0 |
| $\times$ | 1 | 1 | 1 |

$x=$ don't care
Table 5.2. Simplified version of table 5.1

This truth table shows rather more clearly than its predecessor how the SELECT input operates; the $X$ 's in the truth table being, used to denote, the "don't care" states

Thé switch equivalent of a four-way data multiplexer is showri in . Fig. 5.3.

PE47M


Fig. 5.3. Simplified switch equivaient of a four-way data multiplexer

Here the output: Y, can be connected to any one of the four data input lines, A to D, by means of an appropriate input on the two select lines, SO and S1. The truth table for the four-way data multiplexer is shown in Table 5.3. The corresponding Boolean expressions are:-

| Output | Select Inputs |
| :--- | :---: |
| $Y=A$ | $\overline{S 0} \cdot \overline{S 1}$ |
| $Y=B$ | $\overline{S O} \cdot \bar{S} 1$ |
| $Y=C$ | S0. 1 |
| $Y=D$ | S0. S 1 |

We shall now investigate the operation of a practical four-way data multiplexer, the 74LS 153.

| DATAINPUTS |  |  |  | SELECT INPUTS |  | OUTPUT |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| A | B | C | D | S0 | S1 | Y |
| 0 | X | $\times$ | $\times$ | 0 | 0 | 0 |
| 1 | $\times$ | - $\times$ | $x$ | 0 | 0 | 1 |
| $x$ | 0 | $\times$ | $\times$ | 0 | 1 | 0 |
| $\times$ | 1. | + $\times$ | $\times$ | 0 | 11 | 1 |
| $\times$ | $x$ | '0 | $x$ | 1 | 0 ) | 0 |
| $\times$ | $\times$ | 1 | $x^{7}$ |  | $\therefore \quad 0$ | 1 |
| $\times$ | $\dot{x}$ | x | 0 | 1 | 1 | 0 |
| $\times$ | $\times$ | $\times$ | 1 | 1 | 1 | 1 |

$x=$ don't care

## SEQUENTIAL LOGIC

THE 74LS153
The 74LS153 contains two fourway data multiplexers which have common select inputs. The pin connections of the 74LS153 are shown in Fig. 5.4. The two halves of the device


Fig. 5.4. Pin connections for the 74LS153
(referred to as $A$ and $B$ ) are conveniently brought out to pins on opposite sides of the package; the A-side using pins 1 to 7 whilst the B-side uses pins 9 to 15 . Supply connections, using the conventional pins $8(0 \mathrm{~V})$ and $16(+5 \mathrm{~V})$. are common to both halves of the device.

Each half of the 74LS153 has its own active low enable, $\overline{E N}$, input. When these inputs are taken to logic 1 the corresponding outputs immediately go to logic 0 irrespective of the state of
any of the data (DO to D3) or select (SO and S1) inputs.

The internal logic of the 74LS153 is shown in Fig. 5.5. This clearly shows how the $\overline{E N}$ inputs are gated with the select, inverted select, and data inputs at each of the four four-input AND gates on both sides of the device. The outputs of each set of AND gates are then combined in a four-input OR gate. The 74LS153 is effectively nothing more complex than a two-pole fourway switch!

The complete truth table for the 74LS153 is shown in Table 5.4. This truth table is, of course, identical for each half of the device. When both select inputs (SO and S1) are at logic 0 , the output $(Y)$ reflects the state of the DO input. With SO at logic 1 and S1 at logic 0 , the output takes the state of the D1 input, and so on.

The circuit used for our practical investigation of the 74LS153 data multiplexer is shown in Fig. 5.6. It should


Fig. 5.6. Practical arrangement used to demonstrate the action of the 741.S153

| SELECTINPUTS |  | DATA INPUTS |  |  |  | ENABLE | OUTPUT |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| S | S1 | Dø | D1 | D2 | D3 | EN | $Y$ |
| $\times$ | $\times$ | $\times$ | $\times$ | $\times$ | $\times$ | 1 | 0 |
| 0 | 0 | 0 | $\times$ | $\times$ | $\times$ | 0 | 0 |
| 0 | 0 | 1 | $\times$ | $\times$ | $\times$ | 0 | 1 |
| 1 | 0 | x | 0 | x | $\times$ | 0 | 0 |
| 1 | 0 | $\times$ | 1 | $\times$ | $\times$ | 0 | 1 |
| 0 | 1 | $\times$ | $\times$ | 0 | $\times$ | 0 | 0 |
| 0 | 1 | $\times$ | $\times$ | 1 | $\times$ | 0 | 1 |
| 1 | 1 | $\times$ | $\times$ | x | 0 | 0 | 0 |
| 1 | 1 | $\times$ | $\times$ | $\times$ | 1 | 0 | 1 |

## $x=$ don't care

Table 5.4. Truth table for the 74LS153 data multiplexer


Fig. 5.5. Internal logic of the 74LS153

## SEQUENTIAL LOGIC

be noted that only one half of the device is used. In order to provide four different data inputs which may be readily distinguished from one another, DO is fed from the clock whilst D1 and D2 are fed from the Logic Tutor's momentary push buttons, S1 and S2 respectively. The remaining data input, D3, is fed from an inverted clock signal derived from a 7414 inverter. The relevant half of the device is enabled by hard wiring the $\overline{\mathrm{EN}}$ input to logic 0 whilst the two latching Logic Tutor switches, S3 and S4, are used to determine the state of the select inputs, S1 and SO respectively.

The 7414 should be inserted into socket D whilst the 74LS153 should be inserted into socket E with the usual orientation convention (pin-1 of each device to the respective connection marked on the Logic Tutor PCB) being observed. The following links are required:-

| D1 to clock |  |  |
| :--- | :--- | :--- |
| D2 to E3 | (data input D3) |  |
| D7 to OV | (common) |  |
| D16 to +5 V | (supply) |  |
| E1 to logic 0 | (active low enable) |  |
| E2 to S3 | (select input S1) |  |
| E4 to S2 | (data input D2) |  |
| E5 to S1 | (data input D1) |  |
| E6 to clock | (data input D0) |  |
| E7 to D1 | (D1 indicates the |  |
|  |  | output) |
| E8 to 0 V | (common) |  |
| E14 to S4 | (select input S0) |  |
| E16 to +5 V | (supply) |  |

## (A total of 13 links)

The select inputs should initially both be set to logic 0 by appropriate adjustment of S3 and S4. The output indicator, l.e.d. D1, should then be seen to flash 'on' and 'off' in sympathy with the clock which is connected to the DO input line.

S4 should now be adjusted to produce a logic 1 on the SO line whilst S3 remains at logic 0 . In this condition the l.e.d. will stop flashing and become extinguished. Now depress S1 to produce a logic 1 on the D1 input. The l.e.d. will become illuminated whilst S 1 is held down and will become extinguished again when S1 is released.

S3 and S4 should now be adjusted to produce logic 1 and logic 0 on the S1 and S0 select inputs respectively. S2 should now be depressed to produce a logic 1 on the D2 input. The l.e.d. input will become illuminated for as long as S2 is held down.

Finally, S4 should be adjusted to produce a logic 1 input whilst S3 remains at logic 1 . In this condition D1 should be seen to flash 'on' and 'off' in sympathy with the inverted clock. (i.e. when the clock l.e.d. is 'on', the output l.e.d. is 'off', and vice versa). We can summarise these observations as shown in Table 5.5.

| SELECT |  | INPUTS |
| :---: | :---: | :--- |
| OUTPUT |  |  |
|  | SO |  |
| (S4) | (S3) | (D1) |
| 0 | 0 | D0 (CLOCK) |
| 0 | 1 | D1 (S1) |
| 1 | 0 | D2 (S2) |
| 1 | 1 | D3 (CLOCK) |

Table 5.5. Outputs provided by the circuit of Fig. 5.7. (Note: brackets indicate Logic Tutor functions)

## A PRACTICAL APPLICATION OF THE 74LS153

We shall now turn our attention to a simple practical application of the 74LS153 four-way data multiplexer. Let's assume that we wish ta provide digital selection of the output frequencies of a four-stage binary counter. The four $Q$ outputs of the binary counter can be fed to the four data inputs of the multiplexer whilst the two select inputs are fed with a two-bit control signal.

The circuit of a suitable arrangement is shown in Fig. 5.7. 1C1a forms a simple relaxation oscillator in which the output frequency is determined by the time constant, CXR. IC1b forms an inverting buffer, the output of which is a rectangular pulse wave having a duty cycle of approximately 1:2 and a frequency of approximately 32 Hz . This signal is then fed to the CLOCK input of IC2, a 7493 four stage binary counter.

In order to enable the normal counting sequence, the two master reset inputs, MR1 and MR2, are taken to logic 0 and the four Q outputs then have frequencies of $16 \mathrm{~Hz}, 8 \mathrm{~Hz}, 4 \mathrm{~Hz}$ and 2 Hz approximately.

The 7414 and 74LS153 devices should be left in sockets $D$ and $E$ whilst the 7493 should be inserted in socket B checking, as usual, that pin- 1 aligns with B1. The following links should then be made:-
B 1 to B14
B2 to B3
B3 to logic 0
B5 to +5 V (supply)
B10 to E4
B11 to E5
B12 to OV (common)
B13 to E3
B14 to E6
B16 to D4
D1 to logic 0 (via a $47 \mu \mathrm{~F} 25 \mathrm{~V}$ cap)
D1 to D2 (via a 470 ohm 0.25 W )
D2 to D3
D7 to OV (common)
D16 to +5 V (supply)
E1 to logic 0
E2 to S3
E7 to D1 (D1 shows o/p freq.)
E8 to OV
E14 to S4
E16 to +5 V (supply)
(A total of 20 links and 2 components)
The two select inputs should first be set to logic 0 using S3 and S4. The output indicator (l.e.d. D1) should then be seen to flash rapidly 'on' and 'off' with a frequency of approximately 16 Hz . The three other possible settings of S3 and S4 should then be tested.

NEXT MONTH: De-multiplexers and time domain multiplexing.


Fig. 5.7. Simple application of the 74LS153

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# Mono/Stereo Chorus \& Flanger JOHN M.H.BECKER PART TWO 

THE clock signal that causes the delay chips to sample and transfer their charges from stage to stage is produced by 1C9 (Fig. 6). This is a standard linear voltage controlled oscillator chip that produces a squarewave output the frequency of which is related to the value of C24, the current through VR9, and the voltage present on pin 9. The single output from IC9 needs to be split into two opposing phases as required by the delay chips. If a normal phase split were to be given then the opposing edges of the antiphase square waves would coincide. This overlap is prone to causing system noise from the delay chip outputs even though the TDA1097 is basically a low noise device, capable of a 77 dB signal-to-noise ratio at a 100 kHz clock frequency, though this degrades slightly with lower clock rates. The overlap on the edges of the clock is eliminated by the flip flop stage IC10 in conjunction with the NAND gates IC11a-b. C25 and R83 slow down the mutual triggering of the flip flop and gates, resulting in a twin phase output having a short delay between the respective squarewave edges. Oscillograms Fig. 7a to 7c show the 'with' and 'without' effect of the overlap elimination.

Varying the voltage applied to pin 9 of IC9 varies the clock frequency. For the automatic modulation of the clock a constantly varying voltage is produced by the low speed triangle wave oscillator around IC8a-b, and having a frequency governed by the resistance of VR7 and the value of C22. (Oscillogram Fig. 8.) Decreasing either increases the output frequency. The modulation can be switched in and out by S4, and the level varied from nil to full by the depth control VR8. C23 slightly rounds off the triangle peaks at faster modulation speeds. The modulating frequency range is controllable between about 50 milliseconds and 30 seconds, the clock frequency range is between about 12 kHz and 100 kHz . For a single delay chip the delay time range is thus
about 64 ms to 7.68 ms , cascading two delays doubles the delay times. With the modulating oscillator switched out of circuit the unit can of course be used as a standard reverb or short-echo unit, though these effects will not be so pronounced as those obtainable with the September 1984 PE EchoReverb unit.

## POWER SUPPLY

The unit has been designed to operate from two 9 volt batteries producing $+9 \mathrm{~V} / 0 \mathrm{~V} /-9 \mathrm{~V}$, and drawing between 13 mA and 20 mA , depending on the clock oscillator rate. IC2 and IC3 though do not like a total voltage drop across them in excess of 16 V , which also means that controlling voltages must not exceed this either. The positive voltage delivered to IC2,3,9, 10 and 11 is thus reduced to a more suitable level by the drop across the resistor R 62 in the delay line bias divider network. The voltage at $R 62$ is within limits with all i.c.s in circuit, but may rise if any of the said 5 are not in their sockets when power is applied. IC9-1 1 will not mind, but IC2 and 3 may object. The unit may be operated from a stabilised power supply if preferred. The acceptable range is from $+5 \mathrm{~V} / 0 \mathrm{~V} /-5 \mathrm{~V}$ to $+9 \mathrm{~V} / 0 \mathrm{~V} /-9 \mathrm{~V}$. If it is necessary to run from a power supply greater than $+9 \mathrm{~V} / 0 \mathrm{~V} /-9 \mathrm{~V}$ then two voltage regulator devices should be inserted between the power supply and the unit as shown in Fig. 9. The voltage drop across the regulators must be greater than 2 V , and R 62 may be replaced by a link wire.

## CONSTRUCTION

The component layouts for both boards are shown in Figs. 10 and 11. The short link wires on the p.c.b.s can be made from resistor cut-off leads shaped to the correct spacing with thin nosed pliers. Sockets should be used with all i.c.s. The wiring diagram for the unit is shown in Fig. 13. Bring the


PE16276

Fig. 6. Circuit diagram of the Clock Circuit


Fig. 7a. Usual appearance of two square-waves without overlap


Fig. 7b. Close up of overlap


Fig. 7c. Accentuated overlap removal as used in unit

Fig. 7. Clock edge overlap of two anti-phase square-waves


Fig. 8. Modulation oscillator waveform
connecting wires neatly around the edges of the p.c.b.s to the controls. The clock leads to IC2 and IC3 should be brought forward past C19, turn left at the front panel, then along to the small p.c.b., turn right and connect. Do not take them on what appears to be the shorter route across the main p.c.b. as this would direct them across some parts that might pick up any stray radiation signal. Unless you have the


PE16336
Fig. 9. Optional regulator circuit


Fig. 10. Component layout of the Main Board


Fig. 11. Component layout for the Clock Board

## SETTING UP

This is quite straightforward and specialised equipment is not needed. First, VR1 to VR3 midway, VR4 max resistance (anticlockwise), VR5 and VR6 min, VR7 to VR9 max, S1 to S4 off. Plug in a music signal from a prerecorded source into the X 1 socket. Check that the output level reaching the main amplifier used is the same as the original. Switch on S3 enabling the VCA, and bringing up VR6 a change in amplitude and tonal quality should increase. Rotating the clock oscillator speed control VR9 to its maximum resistance will slow down the delay and emphasise the double tracking effect. This will be more apparent with staccato sounds rather than mellow drawn out notes. Adjust VR3 around its midway point until minimum waveform distortion is heard, which will also coincide with the best delay effect. If an oscilloscope is available, the waveform balance will be obvious when monitoring the output at VR1 and VR2 in the presence of a strong input signal. (Oscillograms Figs. 12a and 12b.) Switch on S4 bringing in the sweep modulator. Varying VR8 will vary the modulation depth, and VR7 will vary the modulation rate. Switch off S4, reset VR9 to slowest clock speed, VR6 to maximum level, switch on S2 for feedback enabling. Slowly bring up VR5 and a hollowness to the signal should come in. Maximise VR5 and carefully reduce the resistance of VR4 until the circuit almost goes into full feedback howl. If howl occurs, sharply

Fig. 12a. Sine-wave with VR3 unbalanced but VR1 correct


Fig. 12b. Sine-wave with both VR1 and VR3 correct

Fig. 12. Traces seen at the wiper of VR1



Fig. 14a. Clock residual with VR1 unbalanced (no signal)


Fig. 14b. Clock residual with VR1 balanced (no signal)


Fig. 14c. Sine-wave signal with VR1 unbalanced but VR3 correct

Fig. 14. Traces seen at the wiper of VR1
reduce VR4 and start again. Aim for the closest possible to the howl point. Howl is more likely to occur with strong bass notes. Switch on S 1 to couple the two delay circuits in series and so produce the double emphasis. If necessary back off VR4 slightly as the increase in level may kick the circuit into howl again. If an oscilloscope is not available VR1 and VR2 should be left midway and ignored, otherwise adjust them for the best balance point of the residual clock frequency in the absence of an input signal. (Oscillograms Figs. 14a to 14c.) Switch on S4 and experiment with the various settings until familiar with the control options available, if necessary readjusting VR3 or VR4.

## USE

There are no restrictions to the type of signal fed in provided that the amplitude is less than the distortion level, and that the type of music lends itself to enhancement within the factors discussed earlier and summarised below. It will soon become obvious which type of music requires which particular control setting for the best effect. This is a
matter of personal preference, but the authorfeels that as with any effects unit, moderation is the keyword. Certainly overemphasis of an effect is dramatic, but it is easier to become tired of an over dramatic effect than one which produces a discrete change. In general terms music having a high harmonic content, but otherwise of a simple nature, will benefit most. Mellow or full orchestral sounds will not show the same degree of change. In the first case there is insufficient harmonic information available in the signal for the effect to fully develop. In the second case, the sound is already so full that the effect will probably be lost amongst the tonal complexity unless the original sound is full of spiky waveforms. The harsher sounds of voice, drums, harmonically rich synthesiser and organ music produce excellent effects as the waveforms involved are complex. Pure sine tones and muted waveforms̄, especially in the lower octaves, will be less apparent. For the chorusing effect a slower clock oscillator speed is preferable as the delay time is greater, for flanging, faster clock speeds are better as the phase shift occurs then at a more marked rate and spacing.


Photograph illustrating the internal details of the Chorus and Flanger Unit

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[^3]
# and MICROPROMPT 

## ECONOMIC DIGITISER

Sir-Here is a low cost, easy to make project for use with an $\mathrm{X} / \mathrm{Y}$ plotter, that can be connetted to the expansion interface of the UK 101 , or virtually any other micro.

The system consists of a flexible arm, equipped with two linear potentiometers and a pointer. This pointer moves over a limited surface of $20 \times 20 \mathrm{~cm}$. The voltages, generated by the movement are a measure of the position of the pointer. Those potentials cannot be used directly for $\mathrm{X} / \mathrm{Y}$ plotting, because of their nonlinear output.
A solution of that problem is found, by the application of the formula, which gives the relationship between $\mathrm{X}, \mathrm{Y}$ and the angles of rotation V and H .
If now the analogue values of these angles are translated to digital, the calculation with a BASIC program becomes possible.

The BASIC program can be perceived as a limited loop with continuous conversion, so that the manual movement of the pointer can be digitally stored in memory. It permits also direct writing to a high resolution display.


Table 1 shows a typical BASIC program for illustration, and the following notes apply:

5-30 Initialisation of the PIA (A and B) for input.
VIA (A and B) for output.
40-180 Loop for storing data in memory.
190-280 Loop for playback to X/Y recorder.
If the digitiser is used with the UK 101, it may be used with the PE-Expansion Interface published in Jan-July 1981.
I do not use the internal $\mathrm{A} / \mathrm{D}$ and $\mathrm{D} / \mathrm{A}$ converters, because I wanted a binary indication for the D/A output and also there is only one output in the interface. You will find the schematics joined.

The potentiometers must be of good quality and very linear. A resolution of approximately 2 mm is possible on a surface of $20 \times 20 \mathrm{~cm}$.

During storing in memory, the values of X and Y are continually displayed, and must be integer, positive and between 0 and 255 .

The value of L (line 100 ) is a multiplication constant to certify an optimum sweep between 0 and 255 .

The number 255 (line 110) is added to invert the value of $Y$, which is negative in this area.

Line 50 in the program is the number of points you wish to fix. The movement of the pointer shall not exceed $3 \mathrm{~cm} / \mathrm{sec}$.

Line 255 defines the speed of playback, and

## Prototype digitiser

5 REM : X/Y PLOTTING ROUTINE
$10 \mathrm{P}=61340: \mathrm{Q}=61342$
$15 \mathrm{U}=61344: \mathrm{W}=61345$
17 POKE $+2,255$ : POKE $+2,255$
20 POKER $+1,0$ :POKEP,0:POKEP $+1,255$
30 POKEQ+1,0:POKEQ,0:POKEQ+1, 255
40 INPUT "READY.FOR START";A\$
$45 \mathrm{R}=5000: \mathrm{S}=6000$
50 FOR N=1 TO 200
60 POKER $+1,60:$ POKER $+1,52$
$70 \mathrm{~V}=\mathrm{PEEK}(\mathrm{P}) / 100$
80 POKEQ + 1,60:POKEQ + 1,52
$90 \mathrm{H}=\mathrm{PEEK}(\mathrm{Q}) / 100$
$100 \mathrm{~L}=150$
$110 \mathrm{Y}=\mathrm{L}^{*} \operatorname{Cos}(\mathrm{~V})+\mathrm{L}^{*} \operatorname{COS}(\mathrm{~V}+\mathrm{H}): \mathrm{Y}=$ INT (Y) +255
$120 \mathrm{X}=\mathrm{L} * \operatorname{SIN}(\mathrm{~V})+\mathrm{L}^{*} \operatorname{SIN}(\mathrm{H}+\mathrm{V}): \mathrm{X}=$ INT (X)
130 PRINT X,Y
140 POKER,X:POKES.Y
145 POKEU,X:POKEW,Y
$150 \mathrm{R}=\mathrm{R}+1: \mathrm{S}=\mathrm{S}+1$
160 NEXT N
180 PRINT"END OF LOOP"
190 INPUT" DO YOU WANT A PLAYBACK";B\$
195 IF BS ="Y" THEN 210
200 IF B $\$=$ " $N$ " THEN 40
$210 \mathrm{R}=5000: \mathrm{S}=6000$
220 FOR $\mathrm{N}=1$ TO 200
$230 \mathrm{X}=\mathrm{PEEK}(\mathrm{R}): \mathrm{Y}=\mathrm{PEEK}(\mathrm{S})$
240 POKEU,X:POKEW,Y
$250 \mathrm{R}=\mathrm{R}+1: \mathrm{S}=\mathrm{S}+1$
255 FOR D=1 TO 50:NEXT
260 NEXT N
270 PRINT"END OF PLAYBACK"
280 GOTO 190

Table 1. Suggested software for calculating the angular coordinates

Fig. 1. Mechanical construesion of the digitiser

Fig. 2. Sample of handwriting traced and stored from the digitiser


# MICRO-BUS 

## and MICROPROMPT

depends on the type of $\mathrm{X} / \mathrm{Y}$ recorder (graphic, scope, screen).


Fig. 4. Block diagram of the digitiser


Fig. 5. The ADC channel


Fig. 3. Block diagram of principle


Fig. 6. A plan view showing the geometrics of the digitiser. Good quality highly linear potentiometers must be used to obtain a resolution of around $\mathbf{2 m m}$


Fig. 7. Converting back to analogue for driving a plotter
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# VERTVON al TRZAN Sampe! 

V.T.'s views and opinions are entirely his own and not necessarily those of PE

I'VE JUST had an idea. It doesn't happen all that often. So when it does I like to tell somebody about it.

I've been thinking that as we become more and more a button-pushing civilisation, our ability to communicate with each other, in the way we have been doing since the dawn of mankind, is going to take a nasty knock.

Here's an extreme instance. If and when we reach the stage where we wish our workmates good morning by punching up the salutation on a keyboard-even though we may be no more than an office apart-then sooner or later there can only be one consequence: total atrophy of the vocal chords. There's a lot in the old saying, if you don't use it you'll lose it.

And think what that could lead to in the years after you and I are laid in earth.

The end of live theatre as we know it. The death of opera. The finish of slanging matches in the House of Commons. The demise of spicy revelations at posh cocktail parties. Wholesale redundancy of bingo callers. No more air-cleaning rows between married couples. No more whispered exchanges of sweet nothings between young lovers. The start of mute TV and the passing of radio. The amputation of vocal links with people of other lands... Try that little lot for starters. Of course, cynics will say that out of such evil there comes much good

No more screeching prima donnas. The end of pompous party political gas. The boon of being able to get happily stoned at social functions without having to endure a load of inconsequential chitchat. No more having to bear-though Mum might be upset-the twice-weekly yap of Coronation Street. No more having to study impossible foreign languages. Enhanced matrimonial bliss, made possible by the blessing of mutual silence. Goodbye, the saints be praised, to Russel Harty and Michael Parkinson; and a merciful deliverance from all that is worst in imported American TV.

There's another aspect worth considering, now that we're diving at an ever-increasing pace into the electronic age. How is the keyboard syndrome going to affect the way we educate our children? What, for example, is to be the fate of the good old three Rs?

If you can bear a mioment of near-geriatric nostalgia, let me recall Miss Richardson. She was a grey-haired lady who was totally dedicated to thumping the rudiments of good English into the skulls of her elementary school charges. She had no time for anyone unwilling to share her love of the glories of language and gems of literature. We went
through hell with the old girl. But we emerged with enriched minds.

Then there was old Bandy Andrews. I take off my hat to him as well. He firmly believed that the only worthwhile subjects in the curriculum were simple addition, division, multiplication and subtraction. These were the intellectual vitamins on which he thrived. Anyone who resisted the same diet was beyond the pale.

Finally there was Charlie Atkinson-long since departed for that great big college of calligraphy in the sky. It was he who trained us to express our callow thoughts in splendidly-rounded hands that were a joy to behold. It was his good luck to pass on before the ballpoint pen-which some people feel killed individual style stone dead-came into universal use.

## "We must all accept, indeed embrace, progress as our sires did the wheel."

I agree that our education in those days was pretty elementary. But it had soul and substance. It nurtured the development of latent talents and equipped us for the years ahead. Some of us even got places on the strength of it.

Leaving aside the emotional ramblings, let's look at things in perspective.

The computer, the microprocessor and all their derivatives, with us and yet to come, cannot fail to play an enormous part in our future lives. Nobody but an idiot would deny that. We must all accept, indeed embrace, progress as our sires did the wheel.

But I can't help feeling that we still need the basic support of established educational practices as a preliminary to hurling ourselves headlong into the fresh technologies. There is no substitute for a grounding in the three Rs. Nothing can replace the human larynx as a channel for human understanding.

Someone is bound to say that writing as I do for an electronics journal 1 ought to be more aware of which side my wafer is diffused. Point taken. As I said at the beginning, it's just an idea. But I still reckon that Miss Richardson, Bandy Andrews and Chaplie, Atkinson still have a job to do.

We're all TV critics. Whenever we moan from our armchairs we're carrying out the function, even though it's without an audience or a reward.
I'm no exception. The other night I was watching a programme called "It'll Be Alright On The Night". Presented by that brilliant jester, Denis Norden, it purports to be a collection of rejected sequences resuling from cockups by distinguished performers while recording their programmes.
It is passable entertainment and moderately funny. And, I suppose, acceptable to the gullible. But, because I have that kind of mind, I suspect that some of these boobs are specifically produced in order to provide a relatively inexpensive spin-off. Alright, such conning is perfectly legitimate if it keeps people happy and laughing.

On the other hand, if these lapses from professional standards, which betray a rather irresponsible approach to the job, are genuine, then ought we not to be just a little concerned?
Television is a voracious consumer of time, talent and, above all, money. Money, by the way, which you and I help to provide by passing our crisp oncers across the Post Office counter every year.
Thinking along those lines, it's not easy to accept as a matter of mirth - perhaps even affectionate sympathy-the banalities which such programmes offer.

Sorry Denis. I'm sure it's not your fault.

According to a recent newspaper report, the robots of the future are going to be a lot more cuddly. Apparently 'not tonight darling' will not be a feature of their synthesised vocabulary. Sounds promising.

A spokesman for Cardiff University claims that whispering words of love and affectionate snuggling-up will present no problems for these romantic devices.

Moreover, he promises us, they will be endowded with limitless energy. Sounds even more promising.

But will there be anything in the circuitry to handle that well-known limitation -the headache?

In the meantime, it is reported that America has added a new category to census statistics:-Robots.

The first robot count is underway this month and will be aimed at robots on factory assembly lines. The special census form also has a section to collect information about home robots.

A more frightening rumour is the news that special robots are being seriously considered for duties as "personal" and home security guards. These robots are, it is claimed, programmed to deliver varying degrees of bodily harm; from simple electric shocks to "dismemberment".
It appears that the only obstacle is the expected multi-million dollar lawsuits that could be lodged by injured parties.-A case for Robot against Robot?

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