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SIGNAL GENERATOR F-V CONVERTER

MICROWRITING

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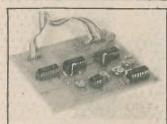
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THIS MONTH'S COVER...

Our cover photograph shows silicon wafers in a furnace during the production of integrated circuits. Photograph courtesy of National Semiconductor.







OUR MARCH ISSUE WILL BE ON SALE FRIDAY, FEBRUARY 1st, 1985 (see page 47)

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8Ω, 0·3W, 2"; 2·25", 2·5", 3"	LEDS price includes Clips	5" LCD ISPLAYS /2 digit 495	VOLTAGE REGULATOR 1A T0220 Plastic Casing	RS	DIL		CDECTDUM
0·3W, 2·5" 40Ω; 64Ω or 80ρ	TIL209 Red 3mm 10 14 14 15 11 12 12 Yellow 14 16 16 16 16 16 16 16 16 16 16 16 16 16	/2 digit 495 digit 530 digit 625	5V 7805 45 p 7905 12V 7812 45 p 7908	55p 55p	8 pin	Low Wire profile wrap 8p 25p	SPECTRUM
DIODES BRIDGE RECTIFIERS	TiL220 -2" Red 12 OI 0-2" Yel, Grn, Amber 14 BF	PTO PX25 250	15V 7815 45p 7912 18V 7818 45p 7915 24V 7824 45p 7918	55p 55p 55p	14 pin 16 pin 18 pin	10p 35p 10p 42p 16p 52p	32K UPGRADE
AA129 20 (plastic case) AAY30 15 1A/50V 18 BA100 15 1A/100V 20	two part clip. R, G & Y 45 Rectangl. Stackable	PW21 320 PX65 320 D74 145	100mA T092 Plastic Casing 5V 78L05 30p 79L05	50p	20 pin 22 pin 24 pin	20p 60p 22p 65p 25p 70p	Upgrade your 16K Spectrum to full
BAX13 20 1A/400V 25 BY100 24 1A/600V 34	Triangular LEDs R&G 18 1L0	275 CT6 Darlington	6V 78L62 30p 8V 78L82 30p 12V 78L12 30p 79L12	50p	28 pin 40 pin	28p 80p 30p 99p	48K with our RAM Upgrade Kit. Very simple to fit. Fitting instructions
BY126 12 2A/50V 30 BY127 14 2A/200V 40 CRO33 250 2A/400V 46	0-2" Bi colour LEDs Red/Green 100 00	Diator 135 L111 70 CP71 120	15V 78L15 30p 79L15 ICL7660 248 LM317K	50p	ZIF TEX	KET	supplied. ONLY £22
OA9 40 2A/600V 65 OA47 12 6A/100V 83 OA70 12 6A/400V 95	0-2" Tri colour LEDs Red/Green/Yellow 85	RP12 78 15777 50 133 135	78H05 5V/5A 550 LM317P 78H12 12V/5A 640 LM323K	99 500	24 way 28 way 40 way	575p . 695p 845p	IDC CONNECTORS (Speed block type) PCB Male Female Female
OA79 15 6A/600V 125 OA81 20 10A/200V 215	High Bright Green or Yellow 100 Sc	n diode 720 hmitt	78HG+5 to LM337T +24V 5A 599 LM723 79HG -2.25V to TBA625B	175 30 75	DIL PL	.UGS (Headers)	with latch Header Card-Edge 2 rows Strt. Angle Socket Connector Pins Pins
OA90 8 25A/200V 240 OA91 8 25A/600V 395	TIL32 Infra Red (emit) 52 OF	РТО	-24V 5A 685 RC4194 LM309K 120 RC4195 78S40	375 160 225	Pins 14 16	Solder IDC 38p 95p 42p 100p	10 way 90p 99p 85p 120p 16 way 130p 150p 110p 195p
OA95 8 BY164 56 OA200 8 VM18 50 OA202 8	TIL78 (detector) 55 Re 50 Re	MITCH flective _139 225	SWITCHES		24 28 40	88p 138p 185p 290p 195p 218p	20 way 145p 166p 125p 240p 26 way 175p 200p 150p 320p 34 way 205p 236p 169p 340p
1N914 4 1N916 5 ZENERS	7 Segment Displays	RS 186	SLIDE 250V TOGGLE 2/ 1A DPDT 14 SPST 1A DPDT C/OFF 15 DPDT	A 250V 35 48	RIBBON	CABLE	40 way 220p 250p 190p 420p 50 way 235p 270p 200p 470p
1N4003 6 39V 400mW	TIL321 5" C.An 140 AL TIL322 5" C.th 140 4× DL704 3" C.Cth 125 4×	UM.BOXES 2 ¹ /2×2" 100 2 ³ /4×2 ¹ /2"103	1/2A DP on/on/on 40 4 pole on of		Ways 10	(price per foot) Grey Colour 15p 25p	SPECIAL 1+ 10+
1N4006/7 7 1N4148 4 1N5401 15 Range: 3V3 to 33V. 1-3W	FND357 or 500 130 5x	4×2 ¹ /2" 120	PUSH BUTTON Spring loaded Latching or SUB-MIN TOGGLE 2 SP changed		16 20 26	20p 30p 25p 40p 40p 65p	OFFER 2764 - 250ns £4.75 £4.35 27128 - 250ns £16.00 £14.00
1N5404 16 1N5406 17 1N5408 19	±1 3" Red or Green 150 5x Bargraph 10 seg. Red 275 5x	2 ³ /4×1 ¹ /2" 90 2 ³ /4×2 ¹ /2"130 4×1 ¹ /2" 99	Momentary 6A SPDT clover 150 SPST on off SPDT cloff	58 85	34 40 64	50p 80p 60p 90p 90p 125p	6116LP - 150ns £3.75 £3.40 6264LP - 150ns £19.00 £18.00
1S44 9 VARICAPS 1S921 9 BA102 30 6A/100V 40 BB105B 40	6×	4×2 ¹ /2" 120 4×2" 120 4×3" 150	DPDT clover 200 SPDT Biased DPDT 6 tags DPDT C/OFF	80	'D' CON	NECTORS:	TRANSFORMERS (mains Prim. 220-240V)
6A/400V 50 BB106 40 6A/800V 65	Crystals 1lb 7×	5×3" 180 6×3" 210 ×4 ¹ /4×3" 240	Non Locking Push to make 15p Push break 25p 4-pole 2 way	Von 185 d 145			3-7 3-0-3V, 6-0-6V 100mA 130; 9-0-9V 75mA; 12-0-12V 75mA; 15-0-15V 75mA. 98p 6VA: 2×6V-5A; 2×9V-4A; 2×12V-0-3A;
TRIACS	DALO ETCH RESIST 10	×7×3" 275 ×5×3" 260	ROTARY: (Adjustable Stop Type 1 pole/2 to 12 way, 2p/2 to 6 way, 3	a) 3 pole/	MALE Solder Angle	80p 110p 160p 24	2×15V-25A 250p
SCR's 3A/100V 48 Thyristors 3A/400V 56 0.8A-100V 32 3A/800V 85	COPPER CLAD BOARDS	×8×3" 295	2 to 4 way, 4 pole/2 to 3 way ROTARY: Mains 250V AC, 4 Amp	48p	Strait	170p 160p 220p 3	10p 24VA: 6V-15A 6V-1-5A; 9V-1-2A 9V-12A; 12V-1A 12V-1A; 15-8A 15-8A; 20V-6A
5A/300V 38 8A/100V 60 5A/400V 40 8A/400V 69 5A/600V 48 8A/800V 115	Fibre Single- Glass sided 6"×6" 100p	Double- sided 125p	DIP SWITCHES: (SPST) 4 way 65 6 way 80p; 8 way 87p; 10 way 10	p;	Solder Angle	105p 160p 200p 33 165p 215p 290p 44	10p 1.5A; 2-20V-1-2A; 2×25V-2A; 2×30V-0 8A
8A/300V 60 12A/100V 78 8A/600V 95 12A/400V 82	6"×12" 175p	225p	(SPDT) 4 way 190p. AMPHENOL CONNECTORS		COVERS		100VA: 2×12V-4A; 2×15V-3A; 2×20V-2-5A; Op 2×30V-1-5A; 2×40V-1-25A; 2×50V-1A
12A/400V 95 16A/100V 103 12A/800V 188 16A/400V 105	21/2×33/4" Clad Plain 'VQ' Boar 21/2×33/4" 95 — 'DIP' Boa	rd 395	24 way IEEE 1DC S	older 470p	IDC 25 w	edge CONNECTOR	965p (60p p&p)
BT106 150 16A/800V 220 BT116 180 25A/400V 185 C106D 38 25A/800V 295	2½×5" 110 — Vero Strij 3¾×3¾" 110 — 3¾×5" 125 95p PROTO-I		24 way Female 490p 4	475p 450p	C-11	2×18 way 210p	Professional DIL SOCKET 8 pin 25p 22 pin 70p
TiC44 24 25A/1000V TiC45 29 480 TiC47 35 30A/400V 525	3 ³ /4×17" 420275p Veroblock 4 ³ /4×18" 590 — S-Dec Pkt. of 100 pins 55p Eurobread	395 dboard 590	ASTEC UHF MODULATORS 6MHz Standard 8MHz Wideband	375p 550p	SIL Sockets 0.1"	2×25 way 285p	16 pin 42p 28 pin 90p 18 pin 47p 40 pin 120p
2N5064 38 T2800D 125 2N4444 130	Spot Face Cutter 150p Bimboard Pin Insertion Tool 185p Superstrip	1 695	ANTEX Soldering trons	535p	20 way 65p 32 way	2×28 way 190p 2×30 way 310p 2×36 way 360p	20 pin 60p JUMPER LEADS
SOLDERCON PINS	VERO WIRING PEN and Spool Spare Wire (Spool) 75p;	380p ombs 6p éa,	G517W G18W	545p 550p	95p	2×40 way 380p 2×43 way 450p 2×75 way 650p	IDC FEMALE RECEPTACLE Jumper Leads 36" 20pin 26pin 34pin 40pin 1 end 160p 200p 260p 300p
ST2 25 500 370p	Wire Wrapping Stakes 100	250p	XS25W	560p			2 ends 290p 370p 480p 525p
COMPUTE	R CORNER		Plastic Library	32-768KH		BBC	MICROCOMPUTER
● EPSONRX80 Printer	ER CORNER	9 [DISC STORAGE CASES	32-768KH 100KHz 200KHz 455KHz		SPECIAL OFFER	RTHIS MONTH ONLY£315
EPSONRX80 Printer EPSONRX80 F/T Printer	£20 ter £21	9 Holds t	DISC STORAGE CASES ten 51/4" Diskettes £1.80	32-768KH 100KHz 200KHz	100 575 370 370 275 275	SPECIAL OFFER We stock the full & Software like, D	RTHIS MONTH ONLY £315 range of BBC Micro peripherals, Hardware bisc Drives (Top quality Cumana & Mitsubi-
EPSONRX80 PrinterEPSONRX80 F/T PrinterEPSONFX80 Printer	£20 ter £21	9 Holds 1	DISC STORAGE CASES	32-768KH 100KHz 200KHz 455KHz 1MHz 1-008M 1-28MHz 1-5MHz 1-6MHz	12 100 575 370 370 275 275 450 420 595	SPECIAL OFFER We stock the full & & Software like, D shi), Diskettes, Pri Covers, Cassette tors (Ready made	RTHIS MONTH ONLY £315 range of BBC Micro peripherals, Hardware plisc Drives (Top quality Cumana & Mitsubi- inters, Printer Paper, Interface Cable, Dust Recorder & Cassettes, Monitors, Connec- (Cables, Pluos & Sockets), Plotter (Graphic
 EPSONRX80 Printer EPSON RX80 F/T Printer EPSON FX80 Printer EPSON FX100 Printer 	£20 ter £21 £31 £42	9 Holds 1 6 Attract leather le	DISC STORAGE CASES ten 51/4" Diskettes .£1.80 DISC ALBUMS	32-768KH 100KHz 200KHz 455KHz 1MHz 1-008M 1-28MHz 1-5MHz 1-6MHz 1-8MHz 1-8MHz 1-8432M 2-0MHz	100 575 370 370 275 275 450 420 595 545 250 225	SPECIAL OFFER We stock the full & Software like, D shi), Diskettes, Pri Covers, Cassette tors (Ready made Tablet) EPROM	RTHIS MONTH range of BBC Micro peripherals, Hardware plisc Drives (Top quality Cumana & Mitsubi- inters, Printer Paper, Interface Cable, Dust Recorder & Cassettes, Monitors, Connec- cables, Plugs & Sockets), Plotter (Graphic Programmer, Lightpen Kit, Joysticks,
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EPSONRX80 Printer EPSONRX80 F/T Printer EPSON FX80 Printer EPSON FX80 Printer SEIKOSHA GP100A KAGA/TAXAN KP81 KAGA/TAXAN KP91 BROTHER HR15 Dais Centronics PRINTEI printers to interface with monitors	ter £21 £31 £42 £12 O Printer £24 O Printer £33 ywheel Printer £32 R CABLE for all the above hithe BBC Micro £19	Holds 1 Holds	DISC STORAGE CASES ten 51/4" Diskettes £1.80 DISC ALBUMS ively finished in beige -vinyl, these convenient- e up to 20 discs. Each disc sily be seen through the lew pockets. ONLY £4.25 51/4" Disc Drive AD CLEANING KIT £12 SPECTRUM	32.768K-1 100KHz 200KHz 455KHz 1MHz 1-20KHz 1-	100 575 575 450 420 595 275 275 450 420 595 2450 420 625 220 625 625 620 62 62 62 62 62 62 62 62 62 62 62 62 62	SPECIAL OFFER We stock the full & Software like, D shi), Diskettes, Pr Covers, Cassette tors (Ready made Tablet) EPROM Sideways ROM B The highly sophis WISE, BEEBCALG Games), BOOKS, tive leaflet. DISC D CS100 — T S, 40 track, 5 CD200 — T 40 track, 5½ EPSON Sir	rTHIS MONTH ONLY £315 range of BBC Micro peripherals, Hardware plisc Drives (Top quality Cumana & Mitsubi- inters, Printer Paper, Interface Cable, Dust Recorder & Cassettes, Monitors, Connec- Cables, Plugs & Sockets), Plotter (Graphic Programmer, Lightpen Kit, Joysticks, loard, EPROM Eraser, Machinecode ROM, sticated Watford's 16K BEEB DFS, WORD- C, Software (Educational Application & etc. etc. Please send SAE for our descrip- RIVES FOR BBC MICRO EC Cased with own Power Supply, S/ 51/4", 100K £119 TEC Twin Cased with own PSU, S/S, 7, 200K £236 Ingle Cased with own PSU, D/S, 40
EPSONRX80 Printer EPSONRX80 F/T Printer EPSON FX80 Printer EPSON FX80 Printer SEIKOSHA GP100A KAGA/TAXAN KP81 KAGA/TAXAN KP91 BROTHER HR15 Dais Centronics PRINTEI printers to interface with monitors	ter £21 £31 £42 £12 O Printer £24 O Printer £33 wheel Printer £32 CABLE for all the above the BBC Micro £19 medium resolution colou £19 S, Green Monitor 40/8	Holds 1 Holds	DISC STORAGE CASES ten 51/4" Diskettes £1.80 DISC ALBUMS ively finished in beige -vinyl, these convenient- e up to 20 discs. Each disc sily be seen through the iew pockets. 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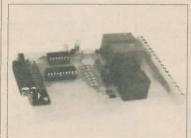
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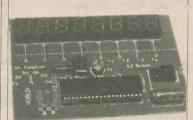
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brightness is required

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test leads, battery, spare fuse carrying case. AC Volts: 0 – 200 – 500 DC Volts: 0 - 2.20.200.1000 OC Current: 0.20m.200mA. Resistance: 0.2k. 20k. 200k. 2M. Size: 138 × 86 × 36mm. (405.202)

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42/mm. AC Volts: 0-200-750. DC Volts: 0-200m-2-20-200-1000. DC Current: 0-20u-2m-20m-200mA 0-10A. Ohms: 0-200-2k-20k-200k-2M, 0-20M, 1405 204) £33.50

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DVM/ULTRA SENSITIVE THERMOMETER KIT

Based on the ICL 7126 and a 3½ digit liquid crystal display, this kit will form the basis of a digital multimeter (only a few additional resistors and switches are readditional resistors and switches are required — details supplied), or a sensitive digital thermometer (50°C to +150°C) reading 0.1°C. The kit has a sensitivity of 200°M for a full-scale leading automatic polarity and overload indication. Typical battery life of 2 years (PP3).



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VOLUME 21 Nº 2 FEBRUARY 1985

SAFETY

LECTRONICS has done much to benefit our way of life and standard of living in all areas from entertainment to safety at sea and in the air. Of course it has also enabled development of more sophisticated weapons and defence systems but that is another story. Our exploration of space is totally dependent on electronics and navigation about our own planet is also now based mainly on high technology.

What a pity then that the modes of transport we all use every day have not benefited more from the introduction of electronics to aid safety. The car you drive may have a computer to show fuel consumption, it may have a talking dash panel or even an engine management computer, but have the electronics been used to improve safety? How many vehicles are fitted with an anti-locking braking system? How often do you see vehicles skidding even on dry roads? How often do the back wheels of unladen lorries lock up when they stop? How many motorcyclists come off in the wet when braking or skid into the back of the car in front?

Admittedly many of the skids that do occur result in no damage or injury but of course some do. Surely it is better to make vehicles safer with an electronically controlled failsafe braking system than to get them talking to you? This is one area where the amateur in electronics can do little himself. We would not encourage readers to modify any

vehicle braking system, so we cannot fit a system to help ourselves.

The sad thing is that the technology and mechanics to perform the necessary tasks has been around for some years. Perhaps the manufacturers feel we will not pay for the extra safety; maybe they do not feel it is necessary? The next time you see a minor skid that could have been dangerous, a motorcyclist fall off, or a lorry stopping slightly sideways just think about what could have gone badly wrong and see if you feel anti-skid braking would be worth another couple of hundred pounds on the already inflated price of a new vehicle in the

LEGISLATION

Maybe you will even think that legislation would be a good thing, even if it might not save as many lives as compulsory seat belt wearing!

Incidentally, the motorcyclist I saw come off this morning was shaken but not badly injured, although his bike was probably a write-off and the car he ran into badly damaged. Think about it if you buy a new vehicle! The extra cost could be worth the time, trouble and heartache alone.

Mike Kenner

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Components are usually available from advertisers; where we anticipate difficulties a source will be suggested.

Old Projects

We advise readers to check that all parts are still available before commencing any project in a back-dated issue, as we cannot guarantee the indefinite availability of components used.

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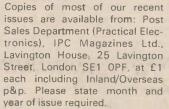
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We regret that lengthy technical enquiries cannot be answered over the telephone.

BACK NUMBERS and BINDERS...



Binders for PE are available from the same address as back numbers at £5.50 each to UK or overseas addresses, including postage, packing and VAT.





Items mentioned are available through normal retail outlets, unless otherwise specified. Prices correct at time of going to press.

BUBUS &

HIGH GOST INSULATION

Most constructors will be painfully aware of the annoying shrink-back properties of insulation, encountered when soldering wires into place. Over the years manufacturers have developed heat-proof insulation materials for specialised cable applications which eventually filter through industry to the home-constructor—and very welcome they are, too. It.may surprise you to know, however, just how far, and to what expense, manufacturers will go in order to optimise the insulating properties of the materials they use.

B.I.C.C. for instance has just completed the installation of a new electron beam accelerator plant at its Electronic Cables factory in Cheshire, the cost? A staggering £2.5 million. The facility is considered to be the most sophisticated and versatile of its kind in the Western world. The accelerator produces high velocity electrons which have sufficient energy to penetrate the cable insulation.

Once inside a polymeric insulation, the electrons initiate chemical reactions which lead to the formation of chemical bonds or crosslinks. Increasing the number of crosslinks leads to eventual formation of a three-dimensional network which substantially enhances the physical properties of the insulant.

The most obvious effect of crosslinking is that the material loses its thermoplastic characteristics and becomes a non-melting



thermoset with a better balance of mechanical properties at both high and low temperatures; chemical resistance is also enhanced

The whole facility is enclosed in 1500 tonnes of concrete for personnel protection during plant operation. The picture shows the plants computer control room.

OBVIOUS

All too often the most worrying aspect for the creator of an original design is, how to protect that idea from those who would copy and exploit it for their own gain. This has been the case since the first inventor brought forth a brainchild, only to stand by helplessly as someone else marketed his idea and made a fortune. The laws governing Patents, Trademarks, Designs and Copyright are complex indeed, without guidance the layman may be forgiven for getting confused. Laurence Shaw's recently reprinted guide can be of great help to inventors and innovators alike.

The Practical Guide for people with a new idea is a book which explains in clear language how to protect a new idea, product or scheme and exploit it to the full. Market research, approaching a manufacturer, telling the world about an idea without losing your rights and patenting an invention are all covered together with secret patents.

This publication is available from booksellers at £5.50, or by mail order at £5.95 from The Patent Eye, George House, George Road, Edgbaston, Birmingham B15 1PG. (021 454 2165).

MAGIC LANTERN

Question: If you are exposed to radiation do you glow in the dark? Answer: Of course not. Not unless you are first coated with a phosphor of some kind. It is a useful fact that beta particles from a radioactive source will, when they strike a phosphor such as zinc sulphide, cause light to be emitted from it. Battelle's Pacific Northwest Laboratories are testing a novel application of this phenomenon. Scientists are evaluating a portable runway lamp for setting up landing strips in out-of-the-way places, or during emergencies in which the electricity supply is lost.

The lamp comprises a glass tube, its inside surface coated with a phosphor, and which is filled with tritium gas, the radioactive isotope of hydrogen. The lamp can not be turned off, it simply continues to glow for the twelve years half-life of the gas. Keeping the glass clean is the only maintenance operation required during that time. The quantity of radioactive material used is so minute that it is harmless even if the glass breaks, it is claimed.

During field tests in Alaska pilots reported that they perceived light from the radioluminescent lamps differently from that of conventional light, and human response now needs to be assessed to find out how useful these lamps may be.

TX TELEVISION/MONITOR

The latest in the TX range from Ferguson is a 14 inch monitor/colour television. It will offer those who can afford a second or even third set a very flexible visual display tool.

The MCO1 has separate RGB, composite video and aerial inputs enabling the user to get the best possible display from broadcast TV, video recorders, teletext and home computers.



Perhaps the most interesting of these options is the ability to directly connect a home computer without the modulation/demodulation problems that occur when using a standard TV set. It must be borne in mind that not all currently available home computers have a direct video output. The machines without this facility have on-board modulation/demodulation and were so designed for use with a visual display medium that most people already possessed—a standard TV set.

The provision of separate RGB, composite video and aerial sockets also allows the home computer, video recorder or game and TV aerial to be connected simultaneously; the set senses the signal selected and switches to it automatically.

A range of special connector leads is available to cover the different home computer options. The set is manufactured in the UK at the company's Gosport plant. It is expected to retail at circa £230.

BT's rumble machine



It's new from British Telecom, For paging far-off staff. A little pocket thing, That could well cause a laugh.

You see instead of 'bleeping', It's been made to 'vibrate'. So you're the only one that knows, HQ and you have got a date.

The waveforms coming through the air, Will go right through your pants. And trigger-off this rumble-box, Like a herd of elephants.

So if you're in a meeting, Friends might still get the rise. When they notice that your eyeballs, Are looking like mince pies.

Ensuring peak response and high-quality reproduction, Electrolube's Video Tape Head Cleaner is a safety solvent designed for use on all magnetic tape heads.

The cleaner loosens and removes accumulated deposits of dirt and tape oxide and dries quickly without leaving any residues on the tape. The cleaner is nonflammable, and non-conductive, it will not damage plastics or rubber.

The solvent comes in handy 110 gram aerosols and is conveniently applied by spraying directly onto the heads and mechanisms. In addition, the cleaner is ideal for spraying onto cleaning tapes and other tape cleaning devices, such as cotton buds or felt and chamois leather sticks.

Available on its own at circa £1.20, or with 25 extra long cotton buds at circa £1.60 from electrical retail outlets.



Following a tongue-in-cheek comment from Mike Cook, the Technical Editor of Micro User, several hundred BBC micro owners recently returned their machines to their respective dealers, in the fear that they were about to detonate.

The unfortunate comment was printed in the magazine's problem page as part of a reply to a reader's query regarding an 'error message'. Mr Cook, believing himself to be the subject of a "wind-up", answered in kind. "Take your computer immediately to the dealer as this error message indicates that it is about to explode."

The manufacturers, Acorn Computers, were not amused, neither was the middle-aged housewife who reportedly surrounded her machine with a bucket of water.

POINTS ARISING...

RING MODULATOR

December, 1984

Alterations to this project must be made as follows:

In Fig. 9 the component marked C35 should be marked R35.

The capacitor C21 should have its +ve terminal connected to R10.

In Fig. 10 the unmarked component mounted between JK1 and JK2 is R47.

A wire link should be connected between JK3 (C25 -ve) and JK4 (C26 +ve).

Please check dates before setting out, as we cannot guarantee the accuracy of the information presented below. Note: some exhibitions may be trade only. If you are organising any electrical/electronics, radio or scientific event, big or small, we shall be glad to include it here. Address details to Mike Abbott.

International Light Show Jan. 14-28. Olympia. E6 British Toy & Hobby Fair Jan. 18-Feb. 2. Olympia. D6 Component Fair March 10. Carleton Community Cntr., Pontefract (on A1 to Darrington). F2 London Medical March 12-15. Earls Court. S2 IFSSEC (fire/security) April 15-19. Earls Court, London. S Cast (Cable & Satellite) April 16-18. NEC, Birmingham F5 Communications April 23-25. Olympia. I Photoworld April 23-May 6. Earls Court. I

CAD April 26-28. Metropole, Brighton. K2

Fibre Optics & Lasers April 30-May 2. Olympia. E Custom Electronics & Design Techniques April 30-May 2. E All Electronics Show/ECIF April 30-May 2. Olympia 2. E Circuit Technology April 30-May 2. E Field Service & Repairs April 30-May 2. Olympia 2. E

Automan (manufacturing) May. NEC. T1

Scotelex June 4-6. Royal Highland Soc., ex. Hall, Ingliston, Edinburgh. A1

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MA MSc CEng MIEE

IN recent years, improvements in semiconductor technology and, in particular, the introduction of a number of highly versatile consumer integrated circuits and power Darlington stages, have resulted in audio equipment which is both compact and very straightforward. This new series deals with the construction of a variety of modules for use in the custom design of sound reinforcing systems and for public address work generally.

We start, this month, with full constructional details of a 50W power amplifier module. This unit forms the basic building block for several complete designs to be described later. Details of suitable pre-amplifiers, line drivers, tone controls and mixers will also be included; the aim being that of affording the individual constructor the widest possible choice of audio system configuration.

THE 50W POWER AMPLIFIER MODULE

The power amplifier module is electrically robust, is simple to construct, and uses low-cost readily available components. In its basic form, the module is capable of delivering a continuous r.m.s. sine wave output of 50W into a 4 ohm load. The design may be easily modified for operation with alternative output transistors and/or supply rails, as shown in

Whilst every effort has been made to avoid the pitfalls, it should be stated at the outset that this project, together with its higher power derivatives, is not for the faint hearted. Indeed, the prototype amplifier was not developed without a few disasters, including four output transistors which literally melted during the testing stage!

An important requirement of this project (and one which readers ignore at their peril) is that the loudspeaker systems employed should be capable of handling the full amplifier output power. However, readers who do not have immediate access to correctly rated loudspeakers need not despair since we shall, next month, be describing a calibrated test load rated at continuous r.m.s. powers well in excess of 100W. A dummy load of this type should prove to be an

invaluable accessory for those wishing to "run-up" the amplifier without destroying their ear drums.

Having started on a cautionary note it is perhaps worth saying that, provided readers carefully follow the setting-up procedure and observe the recommendations concerning heat sinks, component ratings, and supply rails, there should be few, if any, problems.

CIRCUIT DESCRIPTION

A simplified block schematic of the power amplifier module is shown in Fig. 1. The corresponding circuit diagram is shown in Fig. 2. The module consists essentially of a differential input stage followed by a driver and complementary power Darlington output stage. The unit runs from balanced (i.e. separate positive and negative) supply rails with a common OV rail at earth potential.

The input stage is formed by TR1 and TR2 which are connected as a long-tailed differential pair with TR3 acting as a constant current source. The emitter currents of TR1 and TR2 are determined by VR1 which provides a range of adjustment from about 1.5mA to 3.0mA total current. The signal input is applied to the base of TR1, via a switched d.c. blocking capacitor arrangement, whilst negative feedback (both d.c. and a.c.) is applied to the base of TR2. The overall voltage gain of the module is determined by the amount of feedback applied and is approximately equal to the ratio of

	Max. r.m.s. output power	Rec. supply rail voltages	Max. rec. heatsink thermal resistance	TR6 (npn)	TR7 (pnp)	T1 sec. rating 2 ×
I	30W	± 30V	4 deg.C/W	TIP121	TIP126	20V/1.5A
ł	45W	± 30V	2 deg.C/W	TIP141	TIP146	20V/2A
ı	80W	± 40V	1 deg.C/W	10K80	11K80	25V/2·5A
				MJ3001	MJ2501	
1				2N6058	2N6051	
	120W	± 50V	0·5 deg. C/W	MJ11016	MJ11015	32V/3A

Table 1. Output device selection table



CUSTOM DESIGN YOUR OWN HIGH **POWER AUDIO SYSTEM**

AUDIO PROJECT

COMPLEMENTARY POWER DARLINGTON OUTPUT STAGE DRIVER BIAS SUPPLY TR5 INPUT 0 NEGATIVE FEEDBACK PE1556P LOUDSPEAKER Fig. 1. Simplified block schematic of the Power Amplifier Module

R3 to R4.

Direct coupling of input signals is provided by means of S1 which bypasses the d.c. blocking capacitor, C1. In order to preserve symmetry of the differential stage, the following resistors are made equal: R2 and R3, R5 and R6, R1 and R4 (note that the latter assumes that the amplifier is fed from a relatively low-impedance source).

TR4 forms a conventional common emitter driver stage using an npn transistor. Since the quiescent power

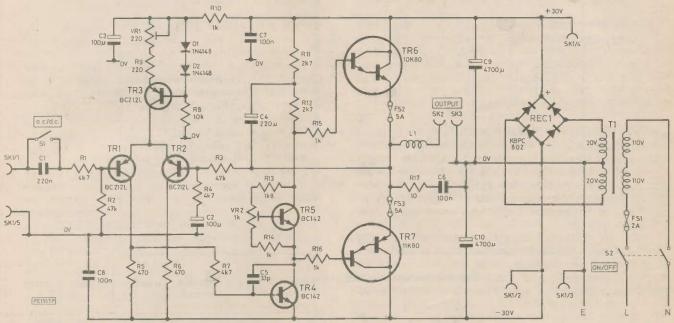


Fig. 2. Complete circuit diagram of the Power Amplifier Module

SPECIFICATION

Maximum power output: 60W r.m.s. into 30hm (measured at 1kHz) 50W r.m.s. into 40hm 40W r.m.s. into 80hm 25W r.m.s. into 15ohm Minimum recommended load impedance: 3ohm Voltage gain: 10 Input voltage for max. rated output: less than 2V r.m.s. Input impedance: 50k approx. Recommended source impedance: 600ohm Total harmonic distortion:

Frequency response (a.c. coupled): 15Hz to 50kHz at -3dB

Hum and noise:

0.05% typical at 30W output into 80hm (d.c. coupled): d.c. to 50kHz at -3dB less than -85dB related to max. rated output

dissipation for this stage is in the region of 125mW, a metal cased TO5 style device is much to be preferred. Bias for the output transistors is provided by TR5 which acts as a constant voltage source, adjustable by means of VR2. The output stage is a conventional complementary symmetrical arrangement using Darlington pairs, TR6 and TR7. A variety of different devices may be employed in the output stage depending upon output power requirements and the available supply voltage rails. These configurations are summarised in Table 1. The output stage is protected by means of two 5A quick-blow fuses, FS2 and FS3. It should perhaps be mentioned that this form of protection is not completely foolproof but will normally cope with a short-circuited load or failure of one of the output Darlingtons.

C6 and R17 form a Zobel network whilst L1 ensures unconditional stability of the amplifier when operating into a severely capacitive load. Bootstrap feedback is applied via C4 in order to raise the effective impedance of the collector load for TR4. C5 provides high-frequency roll-off since the bandwidth of the amplifier is otherwise somewhat excessive. The power supply arrangement is fairly conventional and

provides symmetrical supply rails of nominally +30V and -30V.

CONSTRUCTION

With the exception of the power supply (T1, FS1, REC1, C9 and C10) and the output transistors (TR6 and TR7), all components are mounted on a single-sided p.c.b. measuring approximatly 65mm × 115mm. The component overlay of the p.c.b. is shown in Fig. 3. Components should be assembled on the p.c.b. in the following sequence: terminal pins, resistors, capacitors, transistors, pre-set resistors, fuse clips, and inductor. The latter component consists of 20 turns of 20 s.w.g. wire wound with an inside diameter of 8mm. Care should be taken to carefully remove the enamel at each end of this component in order to facilitate an effective soldered connection to the p.c.b.

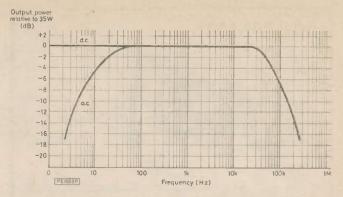


Fig. 5. Frequency response (80hm load)

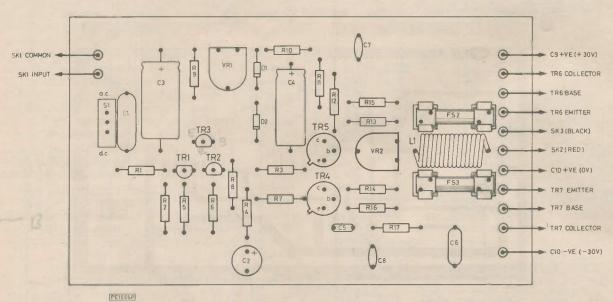


Fig. 3. Component layout of the p.c.b.

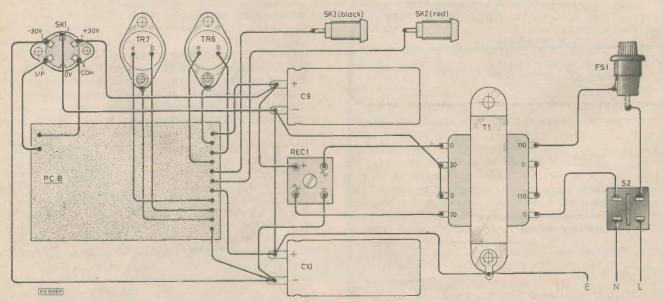


Fig. 4. Wiring diagram for the Power Module

COMPONENTS ...

Resistors

R1,R4,R7	4k7 (3 off)
R2,R3	47k (2 off)
R5,R6	470 (2 off)
R8	10k
R9	220
R10,R14,R15,R16	1k (4 off)
R11,R12	2k7 (2 off)
R13	1k8

R17 10 0.5W 5% carbon VR1 220 min. hor. skeleton pre-set VR2 1k min. hor. skeleton pre-set

Except where otherwise stated, all fixed resistors are 0.25W 5% carbon.

Capacitors

	220h 250 v polyester
C2	100μ 16V p.c. electrolytic
C3	100μ 63V p.c. electrolytic
C4	220μ 25V tubular electrolytic
C5	33p ceramic
C6	100n 250V polyester
C7,C8	100n 100V disc ceramic (2 off)
C9,C10	4700μ 63V can elect. (2 off)

Semiconductors

D1,D2	1N4148 (2 off)
TR1,TR2,TR3	BC212L (3 off)
TR4,TR5	BC142 (2 off)
TR6	10K80 (see Table 1)
TR7	11K80 (see Table 1)
REC1	KBPC802 (200V/6A)

Miscellaneous

p.c.b. s.p.d.t. miniature p.c. slide switch

T1 80VA mains transformer with 220V primary and two secondary windings each rated at 20V/2A minimum (see Table 1)

L1 (see text) p.c. mounting fuse clips (4 off) FS1 2A 20mm quick-blow mains fuse and holder FS2 and FS3 5A 20mm quick-blow fuses

Heatsinks (see text)

Silicone impregnated heatsink washers (thermal resistance $0.33\ deg.C/W$) and bushes (two sets required)

Terminal pins (13 required) SK1 5-pin 270 deg. DIN socket

SK2 and SK3 4mm sockets (1 red and 1 black)

Mains connector

Printed circuit board (502-01)

The Darlington transistors must be mounted on a substantial heatsink of no more than 1 deg.C/W thermal resistance. To facilitate effective heat transfer the use of silicone impregnated washers is highly recommended (it should be noted that the collector connections of the Darlington power transistors are formed by their respective cases and these will have to be insulated from a heatsink which will invariably be at earth potential).

The encapsulated bridge rectifier, REC1, also requires mounting on a heatsink. The requirement for this heatsink is somewhat less stringent than that needed for the output transistors and a rating of 5 deg.C/W (or approx. 110mm x 110mm 16 s.w.g. aluminium) should prove to be quite adequate. Happily, with this component, there is no need for an insulating washer but a liberal application of silicone grease is recommended before assembly. For most practical pur-

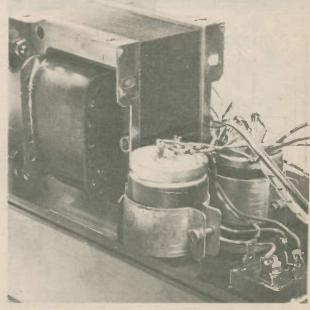
TR1 {c b e	-28·4V 0V +0·6V
TR2 { b e	-28·4V 0V +0·6V
TR3 {c b e	+0.6V +20.8V +21.4V
TR4 $\left\{ egin{matrix} c \\ b \\ e \end{array} \right.$	-1·0V -28·5V -29·2V
TR5 $\left\{ egin{matrix} c \\ b \\ e \end{array} \right.$	+1.0V -0.5V -1.0V
TR6 $\left\{ egin{matrix} c \\ b \\ e \end{array} \right.$	+29·2V +1·0V 0V
TR7 $\left\{ egin{matrix} c \\ b \\ e \end{array} \right.$	-29·2V -1·0V 0V

All test voltages measured with a 20k ohm/V multimeter. **Table 2. Test voltages**

poses the rectifier heatsink can simply be provided by the external case or chassis of the equipment. This expedient will, however, not normally apply to the output transistors unless the case is specially designed with heat sinking in mind!

When the p.c.b. wiring is complete, the underside of the board should be carefully checked for solder bridges and dry joints, whereas the component side should be examined, paying particular attention to the correct placement and orientation of polarised components.

Connections to the heatsink mounted components (TR6, TR7 and REC1) and reservoir capacitors (C9 and C10) should be made by short lengths (typically not more than 150mm) of 16/0.2mm (0.5mm²) stranded pvc covered wire. A typical wiring layout is shown in Fig. 4.

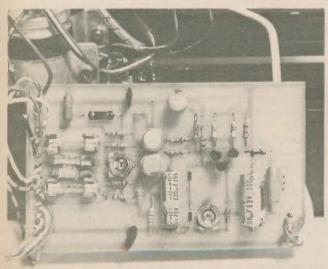


Internal view of the Power Amp

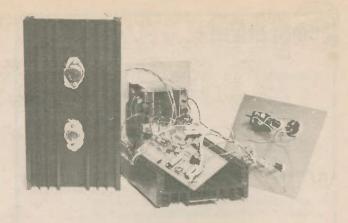
INITIAL TESTS AND SETTING-UP

Before connecting to the mains supply and switching 'on' it is important to observe the following procedure:—

- 1. Adjust VR1 and VR2 so that they are both in the fully clockwise position.
- 2. Switch S1 to d.c. and temporarily short-circuit the signal input connector, SK1.
- 3. Connect the loudspeaker for dummy load described next month). The loudspeaker should have an impedance in the range 40hm to 160hm and should be rated for a continuous power dissipation of 50W.
- 4. Switch 'on' and measure the positive and negative supply rail voltages. These measurements can be most conveniently made using the terminal voltages developed across C9 and C10, respectively. The supply rail voltages, in the quiescent state, should be in the range \pm 27V to \pm 30V. If the voltages differ appreciably, or if FS1 blows on switching 'on', the wiring







of the transformer and bridge rectifier should be carefully checked.

5. Switch-off and disconnect from the mains supply. Temporarily insert two 10ohm 1W resistors in place of FS2 and FS3. This can be done quite simply by trimming and folding back the leads of the resistors so that the body of the resistor is gripped firmly by the fuse clips whilst electrical connection is achieved without the need to solder.

6. Transfer the d.c. voltmeter to the output terminals, SK2 and SK3. Reconnect the mains supply and switch 'on'. Adjust VR1 for exactly OV. If the adjustment has no effect or if the resistors get hot, carefully check the p.c.b. and wiring to the output transistors.

7. Switch 'off' and transfer the d.c. voltmeter to the



10ohm resistor fitted in place of FS2. Switch 'on' and adjust VR2 to produce a reading of 0.2V. Check that a similar reading is obtained across the 10ohm resistor fitted in place of FS3.

8. Switch 'off' and disconnect from the mains supply. Replace FS2 and FS3 and remove the shorting link from SK1. Finally, select normal operation by switching S1 to the 'a.c.' position.

This completes the setting-up procedure and the amplifier is now ready for use. It is advisable to check the adequacy of the heat sinking arrangements by observing the temperature rise of the output transistor after, say, 15 minutes continuous operation at a reasonable output level (i.e. 10W or more). If the rise in temperature is more than 25 deg.C above ambient, the heatsinking should be improved.

NEXT MONTH: We shall provide constructional details of a 100W dummy load and a simple preamplifier/line driver.

Spectrum DAC/ADC Board

R.A. PENFOLD

W ITH something like a million ZX Spectrum computers now in circulation there are, no doubt, a great many in the possession of electronics enthusiasts who would like to use them in computer based measurement and control applications. One of the ZX Spectrum's main shortcomings is a lack of built-in interfaces, and there are no ports ready fitted to the machine that are suitable for applications of this type. However, it is quite easy to fit interfaces onto the expansion port, and an analogue interface is one of the most useful from the electronics enthusiasts' point of view.

The port featured in this article gives both analogue-todigital and digital-to-analogue conversion. Both have 8 bit resolution, which is more than adequate for most practical applications. The analogue output has an output voltage range which is adjustable from 0 to 2.55 volts to about 0 to 10 volts, but with additional circuitry the output voltage range could easily be converted to any desired span within reason. The analogue input has adjustable sensitivity, with the full scale value variable from 2.55 volts to about 25 volts. Again, with suitable additional circuitry practically any input voltage range could be accommodated. The maximum rate of conversion is guaranteed to be no less than 66000 per second, and in most cases in excess of 100000 per second can be achieved. Even the guaranteed rate is fast enough for most high speed applications such as digitising audio signals.

SYSTEM OPERATION

The block diagram of Fig. 1 helps to explain the overall way in which the unit functions. The digital-to-analogue converter is the more simple of the two converters. This consists basically of a precision 2-55 volt reference source, a resistor network (known as an R-2R network) and eight electronic switches. The electronic switches are controlled by the eight

digital inputs, and when activated they connect the precision reference source through to the output via some or all of the resistors in the R-2R network. Things are arranged so that each input, when set high, causes the output to be incremented by the appropriate amount. The operation of this type of converter has been covered in past issues of this magazine, and will not be considered in more detail here.

In order to drive the DAC from the data bus of the Spectrum an 8 bit latch is needed, so that data written to the converter can be stored in the latch and used to drive the inputs of the converter. The converter then gives a continuous output, and ignores signals on the data bus that are intended for other devices. The converter used in this project has a built-in data latch, and it can therefore be fed direct from the computer's data bus. An address decoder circuit provides the latching pulse when data is written to the converter.

The DAC has a 2.55 volt reference source, which sets the maximum output voltage at the same figure. This gives a nominal 0 to 2.55 volt output range in 10 millivolt (0.01 volt) steps. A variable gain amplifier enables higher maximum output voltages to be obtained, up to a maximum of a little over 10 volts. Of course, with a higher maximum output voltage there are still only 256 different output levels, and the output increments in steps of more than 10 millivolts. However, for most applications, such as motor speed controllers and even audio applications, the resolution of an 8 bit converter is at least adequate. The amplifier gives the unit a low output impedance, but without additional buffering output currents of no more than a few milliamps should be drawn.

The analogue-to-digital converter is of the successive approximation type. This incorporates a digital-to-analogue converter which is driven by a fairly complex control logic circuit. The eight outputs of this control circuit constitute the

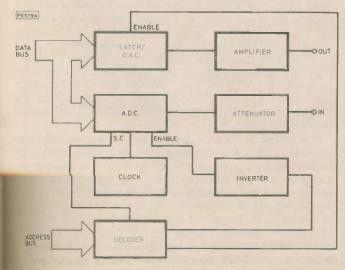
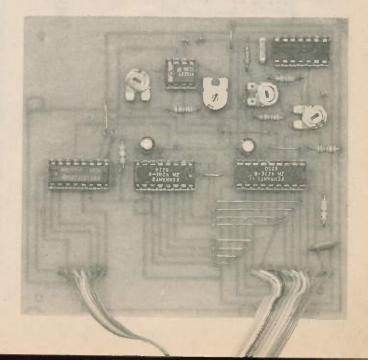


Fig. 1. Block diagram



COMPUTING PROJECT

output of the ADC. The output of the DAC is fed to one input of a comparator, and the input signal is fed to the other input of the comparator. When a trigger pulse is received at the "start conversion" input the most significant bit is set at one, but the other bits are all set at zero. If the output from the DAC is at a higher potential than the input signal the most significant bit is left at one, otherwise it is reset to zero. On the next clock cycle bit 6 is set to one, and, as before, it is either left at one or reset to zero depending on whether or not the output of the DAC is at a higher voltage than the input signal. On the next clock cycle bit 5 is set to one, and the process is repeated with this bit. In fact the same process is used for all eight bits, and at the end of this procedure the 8 bit binary number fed to the DAC is a valid digital representation of the input voltage. This method is reasonably fast, with the conversion taking no more than nine clock cycles, but successive approximation converters are reasonably inexpensive.

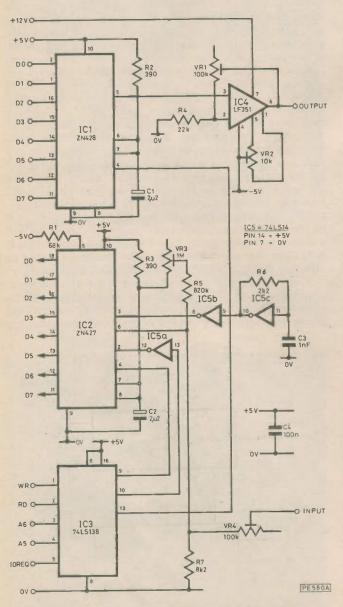


Fig. 2. Circuit diagram of the DAC/ADC board

The device used in this project does not have a built-in clock oscillator, and a simple C-R oscillator is used to provide the clock signal. The "start conversion" pulse is provided by the address decoder. The converter provides its output via an 8 bit buffer which has three-state outputs, and it can therefore be connected direct to the Spectrum's data bus. The "enable" pulse for the outputs is obtained from the address decoder, but an inverter is needed to give a signal of the right polarity. The converter has a nominal full scale sensitivity of 2.55 volts, but a variable attenuator at the input of the unit enables this to be reduced somewhat if required.

CIRCUIT DESCRIPTION

The full circuit diagram of the Spectrum Analogue Board appears in Fig. 2.

All the address decoding is carried out by IC3 which is a 74LS138 3 to 8 line decoder. The Spectrum has a Z80A microprocessor, but it uses a non-standard method of input/output mapping. The general scheme of things is to have the address lines normally high, with one of the lower lines being taken low to activate an input/output device. Some of the upper address lines are occasionally used to provide additional information to an input/output device. This leaves address lines A5 to A7 free for user add-ons. In this case A5 and the IORQ lines are fed to the negative enable inputs of IC3, and A5 must be taken low when reading from or writing to either section of the port (the IORQ line automatically goes low when a BASIC IN or OUT instruction is used).

The three main inputs of IC3 are fed from the read (RD) and write (WR) lines plus address line A6. This gives four usable outputs from IC3, two when reading and two when writing (four outputs are always high since the read and write lines never go low simultaneously). This is adequate for our purposes as only two write outputs and one read output are needed in this application. When writing data to the DAC the instruction OUT 65439,X is used, where X is the value written to the converter. This takes the write and A6 lines low while the value written is present on the data bus, giving an output pulse from output 2 (pin 13) of IC3. Other addresses can in fact be used, but it is best to use 65439 as this places the address lines apart from A5 and A6 high, so that unwanted operation of any internal input/output circuits is avoided.

IC1 is the DAC device, and this is the popular Ferranti ZN428. It has an integral 2.55 volt reference source, but this requires discrete load resistor R1 and decoupling capacitor C1. IC4 is an ordinary operational amplifier non-inverting mode circuit, and this amplifies and buffers the output of IC1. VR1 enables the closed loop voltage gain to be varied from unity to about 5 or so, but in practice the +12 volt supply used for IC4 limits the maximum output potential to about 10 or 11 volts. VR2 is the offset null control, and this is adjusted to trim the minimum output voltage of the unit to zero volts.

The ADC is based on IC2 which is a Ferranti ZN427. Like the ZN428, this has a built-in 2.55 volt reference source which requires a discrete load resistor and decoupling capacitor (R3 and C2 respectively). R1 is part of the high speed comparator, and this is fed from a negative supply so that comparator will respond properly to voltages right down to zero volts. R7 biases the input of IC2 to the earth rail and VR3 plus R5 are used to provide a small positive bias which gives improved accuracy at low input voltges. VR4, together with the input resistance of the circuit, acts as a variable attenuator.

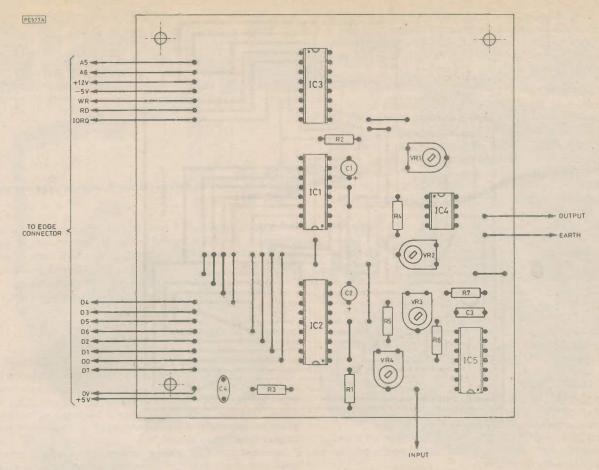


Fig. 3. Component layout of the p.c.b.

COMPONENTS.

Resistors

R1 68k R2, R3 390 (2 off) R4 22k R5 820k R6 2k2 R7 8k2

VR1, VR4 100k 0·1W hor. pre-set (2 off)
VR2 10k 0·1W hor. pre-set
VR3 1M 0·1W hor. pre-set

1M 0·1W hor. pre-set All fixed resistors are 0·25W 5% carbon

Capacitors

C1, C2 2µ2 63V radial elect (2 off)
C3 1nF carbonate
C4 100nF ceramic

Semiconductors

IC1 ZN428E IC2 ZN427E IC3 74LS138 IC4 LF351 IC5 74LS14

Miscellaneous

Printed circuit board (502-02)
2 x 28 way 0-1 inch pitch edge connector
8 pin d.i.l. i.c. socket
14 pin d.i.l. i.c. socket
Two 16 pin d.i.l. i.c. socket
18 pin d.i.l. i.c. socket
Ribbon cable, wire, Veropins, solder, etc.

IC5 is a 74LS14 hex inverting Schmitt Trigger, but in this circuit only three sections of IC5 are utilised. One of these (IC5c) acts as the clock oscillator in conjunction with feedback resistor R6 and timing capacitor C3. IC5b merely acts as a buffer at the output of IC5c. The clock frequency is approximately 600kHz, which is the maximum guaranteed clock frequency for the ZN427. However, with most devices a substantially higher clock frequency is quite acceptable, and where high operating speed is essential using a somewhat lower value for C3 to give a higher clock frequency of up to about 1MHz should give satisfactory results.

The "start conversion" pulse is taken from output 6 (pin 9) of IC3, and is generated using the instruction "OUT 65503,0" (the value written can be any valid quantity since the pulse is obtained direct from the address decoder and not from the data bus). The port is read using the instruction "IN 65503". This gives a negative pulse from output 5 (pin 10) of IC3, but this is inverted by IC5a to give the required positive pulse to IC2.

At least nine clock cycles must be allowed to elapse between sending the "start conversion" pulse and reading the port, to ensure that the circuit has had time to complete the conversion. There is no problem in BASIC since the slow speed of this language means that the conversion will always have been comfortably completed before the port is read. The situation is different when using machine code, and it may them be necessary to use a delay loop to prevent a premature reading of the converter from being taken. The ZN427 has an "end of conversion" status output, but no means of reading this have been included in this unit, and as

the length of time taken for a conversion is virtually constant a delay loop is a perfectly practical way of doing things.

The circuit requires +5, +12, and -5 volt supplies. These are all provided by the Spectrum from its expansion bus, and no other power source is required.

CONSTRUCTION

The component layout of the printed circuit board is shown in Fig. 3. There are a number of link wires and it is probably best to fit these first. 22 s.w.g. tinned copper wire is suitable for the links. None of the integrated circuits are MOS types, but it is advisable to use sockets for these, especially in the cases of IC1 and IC2 which are not the cheapest of devices. The integrated circuits do no all have the same orientation, so be careful to fit them onto the board the right way round.

Connection to the Spectrum is via a piece of 17 way ribbon cable about 0.5 metres long. It is unlikely that 17 way cable will be available, but it is easy to cut down a piece of 20 way cable to the required number of ways. Connection to the board should not prove to be difficult provided the end of each lead first has a small amount of insulation removed and is tinned with a small amount of solder. A 2 by 28 way 0.1 inch edge connector is needed to make the connections to the expansion bus of the Spectrum. Suitable connectors complete with a polarising key are now readily available. Fig. 4 gives connection details for the edge connector.

ADJUSTMENT

Connect the unit to the Spectrum prior to switching on. The Spectrum should then operate normally — switch off immediately and recheck all the wiring if it does not.

Assuming all is well, adjust the DAC first. Set VR1 and VR2 at a roughly midway setting, and then type the following command into the computer:—

OUT 65439,0
This should give a low output voltage from the unit, and by adjusting VR2 it should be possible to trim the output potential to precisely zero volts. Next type into the computer the command:—

OUT 65439,255

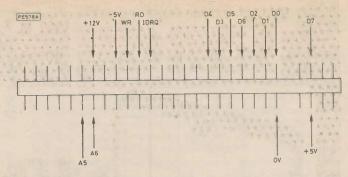


Fig. 4. Connection details for the Spectrum edge connector

An output potential of around 7 to 8 volts should then be obtained. By adjusting VR1 any desired maximum output voltage of between 2.55 volts and about 10 volts or so can be set. Repeat this procedure a couple of times to make sure that everything is set up as accurately as possible.

To check the ADC and facilitate its adjustment type in the following short test program:—

10 OUT 65503,0

20 PRINT IN 65503

30 GOTO 10

When the program is run it should return a series of very low readings (0 or 1). Set VR4 at maximum resistance (fully counterclockwise), VR3 at a midway setting, and connect an input voltage to the unit that is equal to the desired full scale value. This should be in the range 2.55 to 25 volts. Run the program and set VR4 just far enough in a clockwise direction to give returned values of 255.

In order to adjust VR3 an input voltage that produces 5 millivolts at pin 6 of IC2 should be applied to the cirrcuit. In other words an input potential that is 1/510th of the full scale input voltage is required. VR3 is then adjusted to give a series of reading that (more or less) alternate between 0 and 1. It is not essential to carry out this procedure, and accurate results will be obtained if VR3 is simply set for about half maximum resistance.

BAZAAR

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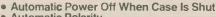
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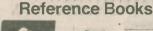
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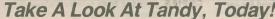




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CABLE Per metre	ving, ties, fixings	22/16 10p	10M 200p	BNC square	D-type rt ang.,skt	FUSEWARE	Range of heat	Round 12"	I TRANS
wire wrap 6p	in stock Phone for	22/2510p	18.432M 270p	skt 100p	15 Wpoa	20mm panel	sinks available -	60W 2862p	FORMERS
Red/white/black	details.	22/3511p 22/6315p	26.54M 200p 26.59M 200p	BNC free skt . 110p	D-type rt ang. skt	holder45p	Phone for quo- tation.	Round 12" 100W4073p	6-0-6 V, 100mA
solid 1/.6	CAPACITORS	22/6315p	26.64M200p	BNC str. adapt.	D-type rt ang, plug	holder59p		Round 12"	167p
11 colours4p Hook-up7/.2	Plate ceramic	47/1611p	26.69M 200p	BNC T adapt. 300p	9 Wpoa	20mm chassis	SPEAKERS	150W 4336p	6-0-6 V. 250mA 185p
11 colours3p	1.8pF - 22nF . 8p	47/25 13p	26.74M200p	VHF piug	D-type rt ang. plug	holder 14p	6V or 12V90p	Round 15"	9-0-9-V
Heavy duty . 32/.2	Disc	47/3515p	26.79M 200p	PL25950p	15 Wpoa	1 1/4" chassis	Ultrasonic 600p	150W7185p	100mA187p
4 colours15p	10pF 10p	47/6324p	26.8M	Small reducer .20p	D-type rt ang. plug	holder17p	transducers	Round 15"	9-0-9 V,
Extraflex	47pF	100/1011p	26.995M 200p 27.045M 200p	PL259 rt.ang90p	25 Wpoa	Line holder 14p	pair	200W 8735p Round 18"	250mA 185p
red/black 15p Tinned copper per	100pF 15p	100/1615p	27.095M 200p	VHF round skt. 50p	Covers 9 120p	20mm fuses	Elliptical 5"x3"	200W £108	12-0-12 V, 50mA 155p
40z reel	1000pF 11p	100/35 19p	27.145M 200p	VHFsquare skt 50p	Covers 15 120p	100mA, 150mA,	198p Elliptical 6"x4"	20017	12-0-12 V
SWG1680p	2200pF11p	100/6325p	27.195M 200p	Ebow adaptpoa	Latches 9 30p	250mA, 500mA,	262p	Motorola piezo	100mA171p
SWG1885p	.01µF5p	220/1615p	27.245M 200p	Straight adapt. 60p	Latches 15 50p	1A, 1.5A, 2A, 3A, 5A	Elliptical 7"x4"	tweeters 2" 231p	12-0-12 V,
SWG20 95p	.022µF5p	220/25 20p	27.255M200p	VHF T adapt. 160p	Latches 25 60p	5A	314p	3 % " 697p	250mA188p
SWG2295p SWG2495p	.047µF8p	220/3523p 220/6333p	CONNECTORS	Female T'	Power plug	fuses 500mA, 1A.	Elliptical 7"x5"	2"x6" horn938p 2"x5" horn796p	0-12/0-12 V. 500mA 369p
En copper per 20z	47 _M F 15p	470/1623p	Croc clips 10p	XLR line plug 180p	2.1mm15p	2A12p	338p Elliptical 8"x5"	2 %" horn 457p	9-0-9 V, 1A . 283p
reel SWG14 70p	Polystyrene	470/25 27p	Terminal post .40p	XLR chassis	Power plug 2.5mm 15p	1 %" fuses 100mA,	5W386p	3¾"624p	12-0-12 V, 1A 350p
SWG1680p	22pF13p	470/3531p	1mm plug 20p	skt	IEC line skt 96p	150mA, 250mA,	Elliptical 8"x5"	,4"x10" 1435p	15-0-15 V. 1A 433p
SWG1890p SWG2090p	47pf8p	470/6348p	1mm socket 15p 2mm plug 20p	XLR line skt 230p	IEC chassis	500mA, 1A, 2A, 3A, 5A, 10A, 13A,	8W521p	Crossovers	20-0-20 V,
SWG2090p	68pF	1000/1024p 1000/1629p	2mm socket 15p	XLR chassis plug160p	plug90p	15A9p	Elliptical 9"x6"	2 way 15W 188p 2 way 100W . 690p	1.5A
SWG24105p	150pF8p	1000/1641p	3mm plug 20p	DIN plugs	IEC chassis skt 90p	1" fuses 2A, 3A,	431p Miniature 1"90p	3 way 25W . 193p	1A
SWG26 105p	220pF 8p	1000/3545p	3mm socket 15p	2 pin 10p	Bulgin P42950p	5A, 13A16p	Miniature	3 way 40W 338p	6-0-8 V, 2A 440p
SWG28105p.	330pF8p	1000/63 75p	4mm plug 15p	DIN plugs	Bulgin P646 . 165p	RESISTORS	1 %90p	3 way 60W 502p	9-0-9 V, 2A . 476p
SWG30	470pF8p	2200/1039p	4mm socket 15p Phono plug 10p	3 pin 15p	Bulgin P430 125p	½ W 5% F24	Miniature	3 way 100W 1346p 4 way 80W . 628p	12-0-12 V, 2A 538p
SWG34 115p	560pF8p	2200/1646p	Phono line skt . 20p	DIN plugs 4 pin 35p	Bulgin P649 135p	E242p	1¾90p	4 way 8097 . 628p	0-12/0-12 V, 2A538p
SWG36	680pF 8p	2200/2556p 2200/3574p	Jack plug	DIN plugs	Bulgin P650 110p	E247p	Miniature 2"90p	0	0-12-15-20-24-30 V.
SWG38 125p.	1500pF8p	3300/2574p	2.5mm15p	5 pin A 15p	Bulgin P635 100p Bulgin P636 130p	1W 5%	Miniature	SWITCHES	2A 900p
SWG40,150p	2200pF8p	3300/3592p	Jack plug	DIN plug 5 pin	Bulgin P551 300p	£12	2¼90p	Toggle Std SPST	20-0-20 V, 2A 745p
Figure 8 per metre 7/.25	3300pF8p	4700/10 59p	3.5mm15p	240°	Bulgin P552 100p	3W www	Miniature 2 % " 8R	Toggle Std DPDT	.30-0-30 V, 2A 933p 12-0-12 V, 3A 721p
Coloured ribbon	4700pF8p 5600pF10p	4700/1674p 4700/25103p	2.5mm15p	360°30p	Bulgin SA2403	2R220p	90p Miniature 2 ½"	DPDT 62p	0-15 V, 3A 647p
per fpot	6800pF 10p	Non-polarised	Jack skt	DIN plug 6 pin 40p	8ulgin SA2404 95p	7W ww30p	64R 100p	Toggle Min SPST 68p	6-0-6 V, 4A538p
10 way 20p	.01µF	1µF25p	3.5mm 15p	DIN plug 7 pin 20p	Bulgin SA2190 50p	10W ww35p	Round 5" 4W 174p	Toogle Min	9-0-9 V, 4A 687p
20 way 40p 34 way 80p	.022µF19p	2.2µF25p	Jack skt line 2.5mm 30p	DIN plug 8 pin 60p DIN skts 2 pin 10p	Bulgin SA1862 50p	25W ww170p Ww Pots.	Round 5" 25W	Toggle Min SPDT70p	12-0-12 V, 4A 845p 0-15 V, 6A 949p
Mains per metre 2	1uF 25p	3.3µF	Jack skt line	DIN skts 3 pin . 20p	Bulgin SA2111	3W High	409p Round 5" 60W	Toggle Min	6-0-6 V, 8A 980p
core Oval 3A 20p	Polyester 49p	4.7μF	3.5mm25p	DIN skts 4 pin . 15p	200p	quality 275p	1587p		12-0-12 V
Round 6A45p	.01uF8p	10 _u F 25 _D	Jack plug ¼"	DIN skts	Bulgin SA2019A 150p	10R 25R 50R 100A, 250R, 500R		Toggle Min DPDT85p	8A 1615p
3 core Round 3A	.015µF8p	22µF35p	monoZup	5 pin A 16p	Bulgin SA2020	1k, 5k, 10k, 50k.	Round 5 %" 10W .	Toggle Min	Toroids: 30VA
Round 6A50p	.022µF8p	33µF 40p	mono20p Jack plug ¼" stereo30p	DIN skts 5 pin B	140p	(M, JA, 10K, JOK.	476p	DPDT c/off117p	6V 950p
Round 13A 80p	.033µF9p	47µF	Jack skt ¼"	DIN skts 6 pin 20p	Bulgin SA2367	SEMICON-	Round 5 %" 15W .	Toggle Min 4PDT209p	30VA 9V 950p
	.047µF9p .068µF9p	100µF70p Thousands of	mono25p Jack skt ¼"	DIN skts 7 pin . 20p	180p	DUCTORS	771p Round 6" 5W 297p	Toggle Min 4PDT	30VA 12V 950p 30VA 15V 950p
Power	.1µF9p	other capacitors in	Jack skt ¼"	DIN line skt	Bulgin SA2368 95p	So extensive is the	Round 6" 60W	c/off244p	30VA 18V 950p
1 mm T&E 40p	.15 _u F	stock i.e.	stereo	2 pin 15p	Many other con-	range of listed se-	1632p	Push to make .20p	50VA 6V 1150p
2.5 mm T&E 60p	.22µF11p	Silvered Mica, 1%	mono25p	DIN line skt 5 pin 30p	nectors, adapters	Please send large	Round 6 %"	Push to break . 20p	50VA 9V1150p
6 mm T&E 150p	.33µF16p	Polystyrene, Poly-	Jack skt line	D-type plug	& leads in stock.	S.A.E. for details.	7W423p	Key sw spst . 259p	50VA 12V 1150p 50VA 15V 1150p
TV COAX40p	.47μF16p .68μF26p	carbonate, Mylar, Tantalum, Trim-	stereo 30p	9 W 80p	OPTO	Transistor mounts	Round 8" 6W 359p	Rotary 1P 12W 62p Rotary 2P 6W .62p	80VA 18V 1200p
Screened Single	1uF	mer, Variable etc.	COAX plug15p	D-type plug	LED Std red 10p.	TO310p	Round 8" 10W	Rotary 3P 4W .62p	80VA 22V 1200p
Twin round	2µF	etc.	COAX skt surf 30p	15 W	LED Std yellow 15p	DIL sockets 8 pin .	Round 8"	Rotary 4P 3W .62p	80VA 30V1200p
Figure 8 min 20p	Electrolytic	CRYSTALS	COAX skt flush25p	25 W 150p	LED Min red 10p	9p	20W963p	Sude min	120VA 30V . 1300p
Figure 8 std 30p	μF/V 1/638p	100k	COAX line skt .45p	D-type skt	LED Min green 18p	14 pin11p	Round 8" 60W 1346p	DPDT22p	160VA 35V . 1500p 300VA 35V . 2000p
4 Core	2.2/509p	1M 600p	COAX coupler . 45p	9 W140p	LED Min yellow 18p	16 pin	60W 1346p	DPDT22p	500VA 35V . 2650p
Spiral wrap 1/8"15p	4.7/639p	2M	CAR aerial	D-type skt 15 W200p	LED clip std 3p	18 pin	10W 700p	DIP 4W 106p	All toroids have
'4"	10/168p	'4M 180p	FM aerial plug 20p	D-type skt	LED clip min 3p.	22 pin 20p	Round 10"	DIP 6W 128p	two isolated se-
%"	10/3510p	4.19304M 320p	BNC plug 100p	25 W 450p	Large range of pa-	24 pin 21p	20W 1113p	DIP 8W 156p	condaries at volta- ges shown.
Wide range of ca-	10/6313p	4.433619M320p	BNC round	D-type rt ang. skt	nel lamphoiders,	28 pin	Round 10" 30W poa	Microswitch 83p	900 31104411
ble markers, slee-	22/108p*	6.144M 130p	skt 100p	9 Wpoa	.de luxe LEDs, etc.	40 pin35n	3014pos	- Country - Cop	Name of the Owner, where



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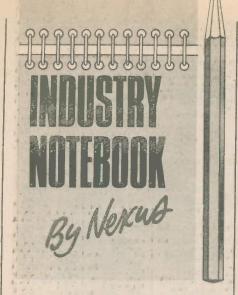
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Outlook

Everyone in business breathed a sigh of relief once the US presidential election was over. The two-year run-up is almost unbearable for its unsettling effect.

All indications, are that 1985 will be a good, though possibly hard year for the electronics industry. In 1983 the number of small companies starting up provided a net gain of 47,000, The 1984 figures, not yet available, are expected to beat this record and there is no reason why 1985 should be worse. A significant number of the new start-ups will be in or associated with the electronics industry.

Foreign investment in the UK continues at a high level. The prolonged miners' strike was apparently seen overseas as a one-off out-of-character industrial relations problem and not typical of the 'new realism' in British industry. In any case no foreign companies would want to invest in coal mining and potential investors may be impressed by the relative ease with which British industry carried on through what was intended to be a crippling exercise.

Expansions and new starts planned last year will begin to take effect. If we look at Scotland's Silicon Glen there are now nearly 300 electronics companies employing more than 40,000 people. Inward investment since the *Locate in Scotland* agency was founded in 1981 has now topped £1,000 million, most of it finding its way into high-tech projects. And substantial investment is similarly going into other areas. Even so they will not create many new jobs, one recent estimate being for 10,000 in the electronics industry this year.

Intense competition in personal computers will force prices down so intending huyers would probably profit by delaying purchase. Alternatively, prices could stabilise but the product improved in the classic "more-bits-per-buck" context. But despite all the difficulties it will still be possible to score well in the consumer market as proved by Alan Sugar's Amstrad whose pre-tax profits topped £9 million in its last financial year.

Information Technology

Information Technology which seemed so novel (although hardly new) only three years ago has now become accepted as the norm and no more exciting than radio or television. Some pessimists are already saying that Britain has been losing ground in this growing sector of industry. Their fears are based on the increase in imported equipment compared with indigenous production.

At the higher levels of the technique the Alvey programme is now gaining momentum. Two new major contracts were awarded towards the end of last year. One carries the painfully contrived acronym of ADMIRAL derived from ADvanced Mega Internet Research for ALvey. The other is merely called the Speech Recognition Project.

The ADMIRAL contract is a £3 million joint venture pelng coordinated by GEC Research Laboratories. Partners are University College, London, The University of London Computer Centre and British Telecom Research Laboratories.

The system will link local area networks (LANS) through a 'mega' internet overlay' to produce a single large system of daţa networks. The key feature is to allow high speed intercommunication between dissimilar equipment. It appears to be a re-jig of part of the Project Universe programme originally initiated by the Department of Trade and Industry and later transferred to the Alvey Directorate.

The voice recognition project is funded with £2 million and is centred on British Telecom Research Laboratories with collaboration from Cambridge University and Logica. Although most schoolchildren are acquiring keyboard skills it is also recognised that speech is the most natural form of communication between people and the same applies between people and computers.

Present voice recognition systems are primitive and generally respond only to single-word voice commands. It is hoped to expand into true verbal dialogue between person and computer so that anyone who can talk can, for example, find what is required from a data base without necessarily having any keyboard skill.

Time for Schools

It is heartening to see that schools are now to be networked through The Times Network for Schools (TTNS) which will give any school access to more than 200,000 pages of information by the end of the year. Secondary schools of which there are 6,500 will be first to join, followed by 27,000 primary schools.

Future plans exist to network British schools to those on the continental mainland. Joining the network will be optional but the fees are modest and the scheme should prove popular and exciting.

Then we have the proposal for a university devoted entirely to information technology. It has the backing of a host of leading electronics companies but students

will have to pay fees to make the university self-financing.

Fears have already been expressed by egalitarians that the university will be antisocial because it will create an elite of the already advantaged who can afford the fees. Nonsense, of course. We need more, not less, centres of educational excellence.

Improvisation

I remember at a press conference organised by a Ministry of Defence electronics establishment asking how we would get on in a real war when the time scale of equipment development stretched over a period of years even when the equipment was comparatively simple. I had in mind the very few weeks which elapsed in 1940 between the alarming discovery that the Germans were using magnetic mines and the countermeasure (degaussing of ships) devised and implemented. And this was only one example of many rapid developments of that war.

I contrasted this with over 10 years of development of the Clansman radio system before it came into service. I was not very impressed with the reply which was more or less that we would probably muddle through as we always had done in the past.

My confidence has now been restored (well, almost) by Alfred Price in his new book 'Harrier & Sea Harrier at War', published by Ian Allan Ltd. In it he describes 'Blue Eric', an electronic countermeasure system needed urgently for the Falklands war. If Harriers were to be operationally successful in the South Atlantic they would need self-protection against Argentine radar installations.

The threat was evaluated from normal military intelligence which already had details of the characteristics of radar equipment in service with Argentine forces. Existing electronic warfare pods (e.g. for Tornadb and Buccaneer) were too large and heavy for the Harrier so it was decided to use elements of the Sky Shadow equipment and fit them in a modified gun pod which would meet the weight and size requirements as well as the Jamming capability.

Marconi Defence Systems were prime contractors and completed the design, testing and delivery of operational units within 15 days instead of an estimated two years at normal pace and at a quarter of the cost.

Blue Eric (named after its MOD project officer Squadron Leader Eric Annal) was never used in the Falklands. When the EW-equipped Harriers arrived they were grounded for four days by bad weather and by the time they got airborne the conflict was virtually over, the Harriers then being used for front line ground attack where the radar threat was negligible or non-existent.

While it is comforting to know that the improvisational skills of yesterday have not been lost, one is still left wondering why an EW pod for Harrier was not already available and why, in peacetime conditions, equipment development times are so long and the cost so great.

Microwriter...

The Principle and the Product

Tom Gaskell BA (Hons) CEng MIEE

HE electronics industry is one of extremely rapid change. New products, ideas, and standards spring up continually, promoting a continuous state of flux and development. As a fairly young industry it is successful in discarding old and outdated principles in favour of newer, more beneficial ones; if change can be shown to be worthwhile in any specific situation, then that change is almost invariably made.

It comes as somewhat of a surprise, therefore, that for the production of documentation, text, correspondence, and computer programs, the primary means of interface between the human being and the machine is still a QWERTY keyboard. QWERTY is the standard layout of typewriter keys which was devised very many years ago with the principle intention of Slowing Down the typist to prevent jamming of the mechanism. In this age of mechanical sophistication and electronic keyboards the same requirement is no longer true since we can easily prevent jamming by other means. Hence, we are left with a legacy from a bygone age. The QWERTY layout is slow and complex to learn, with months of training being required before any proficiency is achieved. For many people such training is impractical, so they are reduced to 'two finger' typing, which is usually a slow and frustrating exercise.

A NEW IDEA

When a company brings-forth a new idea for entering text into machines, it is bound to attract considerable interest. A few years ago a device called the 'Microwriter' appeared. It is a small, self-contained machine with only six keys, which is used with one hand only. The Microwriter company has been producing these devices in modest quantities ever since, and has recently started to advertise and promote the product in a more aggressive way, with various options and accessories now available.

WHAT IS A MICROWRITER?

A Microwriter is no less than a battery powered portable word processor. It is just a little larger than a paperback book and has very few controls—some connectors, an ON/OFF switch, a liquid crystal display, and six keys. It is placed on a desk or held in the left hand, and typed on with the right hand. (As yet there isn't a left handed version since there would be problems connected with the way that the 'alphabet' of letter shapes are formed, as we shall see later.) The Microwriter can communicate over a bi-directional RS232 serial link with printers, full-sized word processors, computers, etc., and can store text either internally on battery backed-up RAM, or on any conventional external cassette recorder.

Characters or numerals are entered into the machine by pressing combinations of keys, rather than one key at a time as in the case of the QWERTY system. There are no markings on the keys since they can have different functions at different times, so the user is immediately forced into the excellent principle of touch typing, and looks at the display rather than at the keys being pressed. The user, therefore, has to learn all the sequences of keys to be pressed before being able to type correctly. This is the make-or-break aspect of the Microwriter—many people are immediately put off by having to learn a potentially complex typing language. Fortunately, the people at Microwriter Ltd. have been very clever indeed in the choice of

keys to be pressed per character. The right hand is always held in the same place above the keyboard, one finger above each key, and the shape formed by the fingers pressing the keys bears a relationship with the shape, or some aspect, of the character which becomes entered into the machine. That relationship is sometimes obvious and direct, sometimes humorous, sometimes very corny, but inevitably is easily memorable. Fig. 1 shows some of these relationships, based on a slightly stylised layout of keys. The manufacturers suggest that they can be memorised in typically one hour, and certainly I have found this to be the case as far as friends, colleagues, and myself have been concerned. It is very easy indeed to learn to Microwrite; far, far easier than touch typing, and I have tried both!

USING THE MACHINE

As each character is entered from the keyboard it is displayed on a single line liquid crystal display which can show up to 14 characters and two control symbols. The display acts as a 'window' on the text, and can be moved around within the text, either following new characters entered or to review what has already been written under the control of special commands. The text, as shown by the display, normally appears to shift to the left as each new character is entered by the keyboard and appears at the right hand end of the display. The sixth key on the Microwriter is a second thumb key, a little below the normal one, and it acts as a control key, allowing comprehensive control of the machine's functions. It is used either on its own, or with other keys in place of the normal thumb key. For example, entering the letter 'f' (the First Four keys pressed), but using the control key instead of the thumb key, moves the display window in the text Forward one position; 'f' for Forward—it is corny, but it works! Doing the same thing with the letter 'k' moves the window backwards. In this case, 'k' stands for Korrect, so you use it when Korrecting errors!





Pressing the control key once, on its own, puts the Microwriter into upper case characters for just one entry, after which it reverts to lower case. Pressing it twice in succession, on the other hand, locks the machine into upper case continuously until the two thumb keys are pressed together to revert to lower case. The status of the machine is continuously shown by two control symbols in a yellow coloured area at the right of the display.

Simple punctuation is provided as part of the normal lower case letter set, but more complex punctuation and numerals have to be accessed by a 'numerals shift' function. Entering the letter 'n', but with the control key pressed at the same time, shifts the Microwriter into the numerals mode for one character only; entering this combination twice in succession locks in the numerals mode, just like the upper case mode. There's another set of character/key relationships for the punctuation, with numbers being entered by a 'count on the fingers of one hand' type of technique. The requirement to shift for numerals is acceptable for word processing applications, but would make the Microwriter somewhat laborious for writing computer programs, for example.

To avoid timing problems when keys are pressed together, the Microwriter works on a key accumulation principle, and the character is only entered when all the keys have been released. Hence, you can start to press keys in any order, so long as at least one of them is being held down at any given time. When all the keys are eventually released, the result is as if all the keys that were depressed in that sequence, irrespective of their chronological order, were pressed simultaneously. This makes the keyboard action very 'forgiving', and allows characters to be entered very slowly and deliberately when required. The speed which can be obtained after only a few weeks' use is very high—not as fast as touch typing, but certainly up to twice as fast as handwriting.

EDITING AND WORD PROCESSING

When text has been written it can be edited (both deletion and insertion) and reviewed by appropriate use of the control key. To read through the written material, the user has to Jump back to the beginning (control + j) then scroll Forwards (control on its own, followed by control + f); this then moves the display window along the text one word at a time, at a user selectable slow or fast rate, until you tell it to stop. The machine automatically enters 'carriage returns' at the end of each line, and ensures that these are between words, not in the middle of them. Via the control key the user can access tabulation, margin indents, document markers, page separators, alter line length, and do many other complex word processor functions. These become very difficult to memorise, and even more difficult to implement, and I would have thought that they would have only limited usefulness to most people.

The control key is also used to suitably configure the RS232 link. Although this can be used to load text into the Microwriter, its primary use is to transmit text to a computer, word processor, or printer from the Microwriter. Full handshaking is provided, and there are user selectable baud rates, data lengths, etc., so it will interface with most RS232 based systems. All settings and text are stored in RAM with battery back-up, so nothing is lost when the power is turned off. The machine even turns the power off itself if it is not used for a few minutes, to



Fig. 1. Sometimes corny, but inevitably memorable

conserve battery life. The batteries are rechargable types, and a suitable charger is provided with the machine. Up to 1600 words, or typically 5 pages of A4 size, can be stored in the memory of the machine. (Much more if cassettes are used.)

THE HARDWARE

The packaging of the Microwriter inspires confidence! It is housed in a very solid injection moulded plastic case. The keys are ultra-low activating-force microswitches with moulded keys. Their action is light but positive, and their positioning is ergonomically spot-on. Inside there is just one main p.c.b. holding the RCA CDP1802A CMOS microprocessor, four HM6116 CMOS 2k Byte static RAMs, and a 2564 8k Byte CMOS EPROM, along with an 'intelligent' liquid crystal display above it as a sub-assembly, and other assorted CMOS i.c.s. The batteries are housed between the microswitches in the upper half of the case. It's a well laid out and professionally built product.

With the Microwriter itself comes a good quality soft carrying case, a battery charger, a cassette recorder connecting lead, some 'crib cards' giving a quick reference to control codes, characters, punctuation, etc., and two instruction manuals; a new user's guide, and a more complex systems manual for setting up communications protocol and the like. The new user's guide is effectively the main instruction manual for the machine, and without doubt is the best manual that I have seen for a piece of consumer electronics. The cartoon characters used might annoy some, but they will drive the points firmly home to just about anybody, whatever age or ability. Other product manufacturers would do well to study this manual and compare its high standards with their own!

There is an optional television interface unit available for the Microwriter which I'm somewhat less happy with. It interfaces to the RS232 port, and allows the display of text on a domestic television set or a composite video monitor. It is expensive (around the £100 mark) and gives very limited facilities. Writing onto the screen as you enter text works reasonably well, but if you just want to dump a letter, for example, onto the screen to check its layout, the use of the Microwriter becomes somewhat more contrived. It's very difficult to put a letter onto the screen without the top of the letter scrolling off the screen as soon as the bottom of the screen is reached. The unit that I tested also failed to get the ends of the lines correct when dumping onto the screen; parts of words were left at the end of some lines, then the whole word reappeared again on the next line. For the majority of potential Microwriter users I would question the necessity for the television interface unit—when you've got the hang of Microwriting you probably don't need it. It seems to be more suitable as a shared facility between several users, and generally seems to be somewhat of an afterthought rather than an integral part of the Microwriter system.

THE QUINKEY

For many people, the cost of a Microwriter (£299 plus VAT), although low by office equipment standards, is too high for them to consider it as a personal purchase. However, they could consider investing in a 'Quinkey'. This appears to be an ordinary Microwriter at first glance, but lacks most of the connectors and the display. In fact, it contains no electronics, just a set of microswitches and resistors which enables up to four of them, ingeniously, to plug into the analogue inputs of a BBC microcomputer. For just under £50 the full Quinkey package provides good value, consisting of the the Quinkey itself, a manual, some crib cards, a connecting lead, and the software to run the system. Further Quinkeys on their own cost around £30.

The software enables the Quinkey to be used as well as the standard BBC QWERTY keyboard, not only with software within the BBC micro such as BASIC, the Acorn DFS, etc., but

also with software packages such as Wordwise and similar. A version for the Spectrum is soon to be made available, and Microwriter are working on versions for other popular personal computers too. All this helps to bring the unique qualities of Microwriting to the private individual, schools, colleges, etc.

APPLICATIONS—WHO USES IT?

The most obvious market for the Microwriter is with professionals on the move—salesmen, executives, engineers, and anybody who does an amount of documentation, report writing, letter writing, etc. On the train or 'plane they can write their meeting reports, or they can keep notes in the field or by their work benches, and either print the results out so that they are legible to themselves and to their colleagues, or if necessary dump them onto the office computer or word processor to be tidied up before final printing. There's no duplication of effort, the typists no longer having to work from handwritten notes.

The small size, portability, and ease of use of the Microwriter are attractions which a QWERTY keyboard has never had. Microwriting can never be as fast as good touch typing, so it will not be used to replace QWERTY keyboards in typing pools or secretarial offices, but for thousands of unqualified typists it offers a refreshing alternative to the two-fingered struggle, so it should be of great interest to small businesses, the police, sales personnel (especially those working from home), budding novelists, and even to the writers of magazine articles! For schools it has the advantage of allowing the connection of four Quinkeys to each BBC microcomputer, which immediately shares out normally limited resources to many more children. If accepted for these applications, it can only help establish Microwriting as a world-wide standard in years to come.

THE FUTURE OF MICROWRITING

Until recent months the promotion of the Microwriter was a very low-key process, although some rather more prominent advertising is now being seen. Over 7000 have been sold, which can only be the very tip of the potential iceberg. I must express reservations, however, about the approach that Microwriter are making on the market place, which seems to be rather uncertain and lacking in self-confidence. I first saw a Microwriter 'in the flesh' in the latter part of 1983, when I had a demonstration and a loan from a distributor for a couple of weeks. I expressed a great interest when I returned the machine to him, and was promised more information and a follow-up call shortly. I never heard from him, or another distributor I contacted, ever again. At the end of January 1984 I approached Microwriter themselves for information and a review sample to help prepare this article. I also ordered two Quinkeys for my own use. I am writing this article in mid August; the review sample only arrived three weeks ago! The Quinkeys arrived in the middle of June, some 19 weeks after they were ordered, and only after telephone calls at the rate of once per fortnight for most of that period. I persevered—I wonder how many others did not?

I hope that the future is very rosy for Microwriting. Amongst friends and colleagues the Microwriter has created more interest than any other piece of equipment that I can remember. The concept of the Microwriter is a work of genius. The market is potentially vast, the product works well, and the presentation is superb. The price is a little high, but should not deter the professional market, with the lower cost market being satisfied by the Quinkey. Let's just hope that Microwriter can improve on the delivery and planning side of it, put some more aggression into the marketing, and produce a commercial, not just a technical winner. What a great shame it would be if the Microwriter concept was lost to an overseas supplier, as has happened to so many other viable products from the UK.

More information can be obtained from Microwriter Ltd., 31 Southampton Row, London WC1B 5HJ. (01-831 6801).

THE LEADING EDGE

DIGITISATION

Everyone talks about the information explosion. The key is digitisation. With digital telephone systems what goes down the line is a series of PCM pulses, rather than analogue waves. Once you have that situation, the sky's the limit.

PCM pulses can carry telephone quality speech, high quality stereo radio, TV pictures, computer data, teletext, viewdata; in fact any information that can be converted into an electrical signal. Switching is by microchip, instead of the primitive Strowger electro-mechanical relay which phone systems have used for the best part of a hundred years.

By interleaving different calls in the same data stream, the capacity of a link goes up around 15 times, i.e. a pair of copper wires that normally carry one analogue telephone call, can carry fifteen digitals. With optical fibres, and the signals carried as light pulses rather than electrons, capacity rises much, much higher.

The British Post Office started working on PCM phone links 20 years ago. Few people know that the PO installed an experimental digital exchange at Earl's Court in 1968 and had it running until 1975. That was when talk about System X started.

Cynics say that the System was called X because no-one really knew what it was going to do or how it was going to do it. Essentially it's a computer switching service for PCM streams and there are now six System X exchanges working in London. One is at Bäynard House in the City of London. The first five were prototypes.

Once data streams are digitally switched and connected, the options available open up wide. There is no problem in providing conference calls, automatically re-directing calls to other numbers or displaying the telephone number of origin when you receive a call.

ELECTRONIC MAIL

Already many people in Britain are using electronic mail, which is a hybrid system of sending digital data down an analogue telephone line. I'm one of them and there are quite a few stories to tell about how the system works in practice, as opposed to theory!

More of that in a future month. At the moment I am trying to find out why the main computer used by Telecom Gold for electronic mail keeps going wrong and leaving users like me stranded!

Why worry about information technology? There's a very short answer. It is always far cheaper to send electronic data down a telephone line, or over a wireless link, than shift people or bits of paper from town to town or country to country.

The best example of this is what happens at the *Economist* magazine. This London-based publication also prints in America and the Far East. Printing master plates are sent by airline courier to the Orient. Until a year ago they were also sent to America.

The plum job on the *Economist* was to take a day trip on Concorde to New York and back, with the print plates, for safe keeping. Now the magazine text is converted to digital data and sent by satellite direct to a Connecticut printing works, which publishes virtually simultaneously with London.

Wisely the *Economist* still sends a back up text by 'plane just in case the satellite link breaks down. But no-one gets the plum job of going along with them any more.

VIDEO NEWS

Polaroid has joined Kodak in 8mm video. Sony may follow next year but so far everyone else is sticking with their existing VHS and Beta formats. Ironically by joining Kodak, Polaroid may well have helped its rival succeed. The extra name gives the new format credibility.

At the Chicago Consumer Electronics Show both companies were demonstrating NTSC camcorders using the 8mm cassette. Picture quality was good and sound, using f.m. mono, seemed OK. The big question mark is over tape supply.

Video writing speed is very low; 3.8 metres a second for NTSC and 3.1 metres a second for PAL and SECAM. So packing density must be very high. You can get it either from tape coated with metal powder (MP) and coercivity around 1600 oersted. But this needs video heads which are expensive and may be short lived. The other way is to use lower coercivity tape coated by evaporation of cobalt-ferric metal in a vacuum (ME). No one has yet succeeded in making ME tape reliably in bulk.

Kodak started shipping 8mm camcorders to US traders last September. A 90 minute cassette costs \$24 and the system \$2000. There is no sign yet of a PAL or SECAM prototype. Although 8mm video almost certainly comes too late and too expensive to catch the domestic market, it could well form the basis of a new professional camcorder format.

Sony has both domestic and pro interests. Kodak and Polaroid are paying Matsushita, Toshiba and TDK to get the technology right for domestic use. Professional use is the logical follow on.

CLEAN CUT

I have now seen inside several compact disc and videodisc manufacturing plants in Britain, Germany and Japan. They all have one thing in common with a microchip factory, that is absolute cleanliness.

Exactly the same situation exists in magnetic tape factories, where any dirt in the atmosphere will end up as non-magnetic blemishes in the coating and cause dropout.

Air in the so-called "clean areas" is filtered to Class 100, that is to say less than 100 particles of less than 0.5 micron size in every cubic foot of air. The pressure of air inside these clean areas is higher than the atmosphere outside, so when a door opens clean air blows out and dirty air leaks in.

The staff must wear full length lint-free jump suits, like space clothing, and only a few visitors are allowed in. Usually there is an air shower, where blasts of clean air flush dirt, dust, dead skin and dandruff off every human passing through.

If only, I think every time I visit one of these plants, factories which press ordinary records would take even remotely comparable steps to preserve cleanliness. The official answer is that it's not necessary.

Certainly, by comparison, the technology of LP production looks like a blunt instrument. But it is easy to forget that a vinyl LP record is by far the most precise product mass produced from plastics!

The groove of an LP record is specified by IEC standard to be never less than 25 microns (or millionths of a metre) wide and preferably not less than 35 microns wide. As a "yardstick" a human hair is around 50 microns in width. The IEC puts stylus tip radius at between 15 and 18 microns.

Now let's look at a Laservision videodisc, and a compact disc digital audio record. Both have a spiral of information pits with a track pitch of 1.6 microns.

For videodisc the pits are 0.5 microns wide, and for compact disc they are 0.6 microns wide. Video pit depth is 0.1 micron and CD depth 0.12 microns.

In other words there is very little difference in the dimensions; both are at least 50 times smaller than the LP groove. The laser spot for videodisc playback is focused to a circle of 0.9 micron diameter and for compact disc it is 1 micron. The layer of protective lacquer in a compact disc has to be exactly 1.2 millimetres thick, or, it will affect the laser focus.

PARTY TURN

If you collect useless information to bring out of the bag at boring cocktail parties, here's one for the bag. A CD player rotates the disc at a speed which varies between 3.5 revolutions a second, a give a constant tracking velocity of 1.25 metres a second.

That means that for a one hour disc there are 4.5 kilometres of track on a single side. For a laser videodisc the track length is 31 kilometres!

BARRY FOX

TERMS OF BUSINESS

- * All prices exclude V.A.T. and carriage. Please add carriage to order total before adding V.A.T.
- * Carriage charges extra on all orders as follows: ٤0.75 Components Books/Data/Software £2.00 Printers, Monitors, Disc drives, etc.
- * Strictly cash with order or credit card (Access or VISA) only.
- * Delivery is normally from stock but please allow up to 28 days.
- * Any guery or complaint regarding an order should
- * Goods incorrectly ordered cannot be accepted for replacement without our prior agreement. Due to high processing costs, a minimum of 15% handling charge may be levied on any returns or cancelled orders.
- £4.50 * We will issue a full immediate refund, if requested, for out of stock items.
 - * All items carry full manufacturers warranty.
 - * A V.A.T. receipt will be supplied with all orders.
 - * Prices quoted are correct at the time of going to press but we reserve the right to effect changes



	8086	MEMORIES - EPRO	MC	75173N 75174	1.44 2.82	F.D. CONTROLLERS		74116	251N 1.03	74LS22 74LS221	0.17 4033 0.62 4034	2. 40 4078 1.00 4081
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309P 6.25	82C88 16.80	4164-150ns 4416-200ns	4.45	LM301AN LM308AN	0.30	ZN429E-8 ZN432CJ-10	20.79	74F194 1.68 74HC	4538 2.36 4543 3.04	741528	1.00 4068	0.50 4526 0.16 4527
310 1.70 321 1.70	Z80	4532-200ns	2.45	LM308N	0.56	ZN432E-10	13.00	74F20PC 0.52 74HC	51N 0.64	174LS290	0.29 4069	0.23 4528
	FAMILY	4564-150ns 8118-100ns	1.45	LM311N LM317MT	0.60	ZN433CJ-10 ZN434	25.00	74F240 3.16 74HC 74F241 2.42 74HC	533N 2.40	74LS293	0.29 4070 0.17 4071	0.23 4532 0.23 4541
845 6.45	Z80ACPU 1.99	81256-150ns	25.00	LM317T	1:06	ZN435	4.38	74F243 2.80 74HC	589N 1.72	74LS32	0.25 4072	0.23 4543
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3.70	Z80BCPU 5.95	*ZERO POWER ZK		LM350T	3.12	ZN449	2.72	74F280 1.74 74HC	76N 0.64	74LS373	0.17 CRYST	1MHz
3B40 6.60 3B50 1.58	Z80BCTC 5.95	CMOS*		LM358N	0.60		22.50	74F283 1.74 74HC	85N 2.02	74LS374	0.52 41174	1.008MHz
3B54 7.95	Z80BPI0 5.95		32.00	LM3900 LM393N	0.68	ZNA234E	9.40	74F32PC 0.52 74HC 74F352 1.26 74HC	86N 0.80	7415375	0.26 A113A	1.8432MHz
	Z80BSIO-119.95	MK48Z02B-200ns	24.00	LM725CN	3.00	VOLTAGE REF.		74F353 1.26	00414 0.00	74LS378	0.46 A116A 1.22 A120B	2.4576MHz 4MHz
		MK48Z028-250ns	23.00	741CP LM747CN	0.16		0.50	74F373 3.16 TTL 74F374 3.16 7415		74LS379		6MHz
- [Z80SI0-3 6.00 Z80SI0-1 6.00	BIPOLAR PROMS		LM748CN		ZN423	0.98	74F379 1.83 74L5	00 0.17 01 0.17	74LS38 74LS386	0.25 A140A 0.50 A160A	8MHz
	Z80SI0-2 6.00	TBP185030N	1.54	MC1413P		ZN458	0.92	74F301 0.02 741 F		74LS390	1.10 01730	3.6864MHz 9.8304MHz
805 FAMIL		TBP18SA030	1.38	MC1416 MC14411	0.80	ZN458A ZN458B	1.12	74F302 4.22 74LS	0.17	741540	0.52 A182A 0.25 A182A	19.6608MHz
C1468052P	12.60	TBP24S10N TBP24S41N	2.06 6.68	MC14412	14,20	ZNREF 025	1,90	74F399 2.70 74L3		74L542	0.25 0.30 DIL SK	TS TINI
C146818P	7 20	118P24581N	5.50	MC1458CPI MC1495L	0.35	ZNREF 040 ZNREF 050	1.90	74F533 3 16 74LS	0.17		0.30	1+
C146823P	8.80	TBP24SA10N TBP24SA41N	1.40	MC1496P	0.70	ZNREF 062	1.90	74F534 3.16 74LS		741 540	0.34 0707080	02 8 PIN 0.07
C68705KT3 C68705R3L	40.00	[[BP 28	3.10	MC1723P		ZNREF 100	3.05	74F537 6.02 74LS		/4L551	0.17 0707140	
C68705U3L	36.00	IBP28LA22N	4.14	MC3242A MC3302P	6.30	BUFFERS		74F539 4.38 74LS	11 0.17	741555	0.17 0707160	02 16 PIN 0.09 02 18 PIN 0.15
8000 FAMI		TBP28S166N T8P28S42N	4.50	MC3340P	4.30	81LS96	0.00	74F64PC 0.52 /4LS		74LS670	2.30 0707200	02 20 PIN 0.19
C68000G10		TBP28S46N TBP28S86N	4.50	MC3357P MC3423PL	1.90 0.81	811597	0.80	74F86PC 0 77 74LS	114 0.44		0.30 0707220 0.35 0707240	02 22 PIN 0.21 02 24 PIN 0.24
C68000L8			5.00 4.50	MC3441AP	2.90	81LS98	0.80		12 0.25		0.2810707280	02 28 PIN 0.26
C68008L8	45.00	TBP28SA46N	4.50	MC3446AP	2.90	8T26A 8T28	0.80		122 0.42 123 0.53	74LS76	0 401	02 40 PIN 0.29
C68230L8 C68451L8	19.50	TBP28SA86N AM27S13PVC	8.62 3.74	MC3447P MC3448A	4.30	8T28A	0.80	SPEED 74LS	124 2.30	7/1 583	0.19 0.28 DIL SK	TS GOLD
C68901P	75.00	AM27S19PC	1.92	MC3470P	6.44	8795	0.80	CMOS 74LS	125 0.49 126 0.29	74LS85	0.39 0606080	02 8 PIN
9900 FAN		AM27S191DC	15.00	MC3480 MC3487	7.76 1.80	8T97A 8T98	0.80	74HC00N +0.42 74LS	13 0.17	741500	0.42 0606140	02 14 PIN
159901-95		AM27S25DC AM27S29DC	15.00	NE555P	0.25			74HC02N 0.42 74LS	132 0.73	7/11 5/01	0.21 0606160 1.30 0606180	02 16 PIN
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components GILRAY ROAD, DISS, NORFOLK, TEL: 0379 4131

INSULATION DIS				
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40 way 2.28 50 way 2.70	2.54 1.67	50 way 5.36	24 4.18 4.36	4.55
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	26	0.35 0.62 0.45 0.80	5 WAY DIN SKT 180° 5 WAY DIN SKT DOM	0.90
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POWER OP-AMPS (TCA365 and TCA2365)

ONE of the most important components available to the analogue circuit designer is the operational amplifier, or 'op-amp'. The majority of these, however, are somewhat limited in their load driving capabilities. Simple devices such as the 741 can only output 25mA under short circuit conditions, or 10mA in normal operation. For much higher currents it is usually necessary to add extra driving transistors to a conventional op-amp.

The TCA365 and TCA2365 are power opamps which allow the designer to use a single i.c. in high power applications rather than the more cumbersome 'op-amp plus components' approach. In practice, they behave as fairly ordinary op-amps with the exception that their output stages can drive up to 3 amps in the case of the TCA365, or 2.5 amps per amplifier in the case of the dual op-amp TCA2365. The two i.c.s are very similar, with both sets of specifications being given in Fig. 2. The main points to watch are supply voltage maxima, output currents, and power dissipation; these all vary between the 365 and the 2365. (Note that the output current shown for the TCA2365 is 2.5A per amplifier, not for the whole i.c.) Fig. 1 shows the pinouts of the i.c.s. For moderate to high power applications, heatsinks should be used. These should be insulated from the i.c.s' tabs if the internal connections to the -ve supply could cause short circuits or problems.

The TCA2365 has an 'inhibit' input which can be used to turn the outputs of the op-amps off, ie. high impedance (approximately 4k). Inhibiting is effective when pin 6 is taken to the —ve supply rail, and the amplifiers operate normally when pin 6 is taken above 3.0V referred to the —ve supply, or left unconnected. Both the TCA365 and the TCA2365 have extensive protection; they are d.c. short circuit proof and have thermal overload and safe operating area protection. The internal current limiting makes them ideal for driving complex loads, and especially for driving filament lamps, whose low resistance in the 'cold' state can cause problems with other types of driver.

BASIC CIRCUITS

Some basic circuits for use with these power op-amps is shown in Fig. 3. In all cases there is an external Zobel network (sometimes known as a Boucherot network) fitted between the output and 0 volts to help to maintain stability under widely varying load conditions.

The 1 ohm resistor does not have to be high power ($\frac{1}{3}$ watt will do) and the capacitor must be 100nF for the TCA365, or 220nF for the TCA2365. It is unimportant which way up the network is fitted; the capacitor can be connected to 0V and the resistor to the output, or vice versa. Both power op-amps can be used with either split or single rail supplies, just as would be possible with most conventional op-amps.

Figs. 3a and 3c are very straightforward conventional op-amp circuits, and apply perfectly well to the TCA365 and TCA2365. For minimum offsets, Rg in Fig. 3a and Ri in Fig. 3c should be included as shown, although in many circuits these are unnecessary and can be replaced by short circuits for economy. Both these circuits, however, should really only be used for higher gain circuits; +10dB or more, or preferably +20dB. For lower gain circuits, and certainly for anything less than 10dB (approximately ×3), the configurations of Figs. 3b and 3d should be used. For unity gain, use typically between 10k and 100k for both Ri and Rf, with Ro approximately one tenth of that value, in Fig. 3b, and typically between 10k and 100k for Rf in Fig. 3d, with Ro one tenth of that and Rg an open circuit. The reason for all this is concerned with stability.

STABILITY

There are many factors influencing stability in operational amplifiers. These tend to be involved, complicated, steeped in complex-plane mathematics, and certainly beyond the scope of Semiconductor Circuits! Empirically, most electronics engineers and enthusiasts learn some straightforward rules of thumb about how to keep amplifiers stable and prevent problems of self-oscillation at several megahertz. A common 'cure-all' is to connect a small value capacitor, typically less than 100pF, between the output and the inverting (-ve) input. Don't do this to a TCA365 or 2365! Even if it doesn't actually cause oscillation (which it probably will) it will certainly make oscillation much more likely. This is basically due to the fact that the opamps have poor stability at low gains, and a capacitor across the feedback loop ensures low gains at high frequencies. For gains of more than 20dB (x10 gain) the i.c.s are normally quite stable, assuming that the Zobel network is fitted and that P.S.U. decoupling is taken care of. More than 10dB (x3 gain) is normally acceptable, but below this there can be problems with transient response

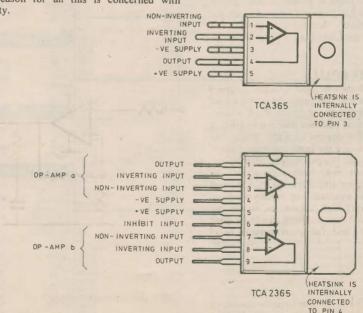


Fig. 1. Pin outs for the TCA365 and TCA2365

EVERY METALLY AND		1 1 2 2 1 1	, comgre c)p-Amp)	TCA23			
Characteristic	Notes	Minimum Value	Typically	Maximum Value	Minimum Value	Typically	Maximum Value	Units
Supply voltage	All spec's quoted at ±15V for	±4	±15	±18	±4	±10	±13	V
a many la	TCA365 and $\pm 10V$ for TCA2365	*(or 8V)		*(or36V)	*(or 8V)		*(or26V)	P. S.
	(In normal operation:		20	40	_	30	50	mA
Quiescent current	with amps inhibited:	A TOTAL BA	CATE OF THE PARTY	TON THE LOW	and service	5	8	mA.
_	(TCA2365 only)	11/2/1/2		2 154			176 37 6	
Temperature range		0		+70	-25		+85	°C
Maximum O/P current	Per amplifier			3.0	35/		2.5	A
Maximum I/P voltage	(Differential)	10		Supply rails		The state of	Supply rails	
I/P offset voltage		-10		+10	-10		+10	mV
I/P offset current	1011	-0.2		+0.2	-0.1		+0.1	μΑ
Temperature coefficient	(Of input offset current)		0.0	0.1		0.05		nA/°C
Input current	A. 4511-		0.2	1.0	4.0	0.25	1.0	μА
Input resistance	At 1kHz	1100	11100		1.0	5		MΩ
Output voltage	Load resistance = 470Ω at Load resistance = 4.7Ω 1kHz	±13.0	+13.2	86 100				V
Slew rate	Load resistance = 4.752 TKHZ	±11.7	±12·0	-	±8·0	<u>+8.5</u>		31/
Voltage gain	Open loop, at 100Hz		90		70	80		V/μs dB
I/P common mode	Open 100p, at 100112	+13.4	+13.5	- cr	+7.0	+7.5		ab
voltage range	Load resistance = 470Ω	-15.0	-15.0		-10	-10.5	CONTRACTOR	V
Common mode		4			-10	-10.5	1000000	
rejection ratio	Load resistance = 470Ω	75	83	EAD-	70	80		dB
Supply voltage	Gain = x100, frequency = 20Hz	50	62	7 (12	SE TOPE			
rejection ratio	Gain = $\times 10$, frequency = 100 Hz	30	02		70	80		dB
Power dissipation	Total for package, at 90°C	2		15.0	70	00	6.0	W
Equivalent I/P noise	Gain = $\times 11$, I/P resistor = $10k$			100		3.0	0.0	μV
Inhibit input	For i.c. turned off	1 . 3 / [. 11]		-	0	0.0	1.0	V
							(+ve	
(TCA2365 only)	For i.c. turned on	14		-	3.0		supply)	V

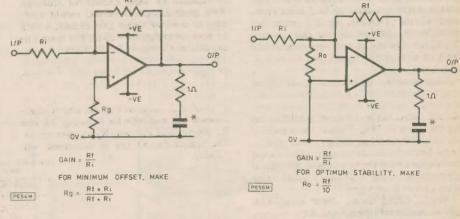
Fig. 2. Specifications (note different supply rails used in measuring spec's.)

(overshoot of the output on square waves) and stability,

Hence, the circuits of Figs. 3b and 3d should be used for low gain applications. Although the actual voltage gains of these circuits are exactly the same as the equivalent gains of Figs. 3a and 3c, the inclusion of Roactually causes the op-amps to be working in a 'high gain' way. Normally, this is rather undesirable, since there is no apparent benefit to the user and the amplifier has a much noisier output voltage, but in this application the 'pseudo gain' helps to ensure stability at low real gains, and is to be recommended for use with any circuitry demanding a gain of less than ×4, or even less than ×10 to be on the safe side.

POWER SUPPLIES

The capabilities of these op-amps to dump several amps from the supply rails into a load puts considerable strain on the P.S.U.s used. The best general guidance that can be given is to consider the devices as audio power amplifiers, and to use the same constraints about removing earth loops, supply decoupling, keeping inputs away from outputs, etc. As with audio power amplifiers, the TCA365 and TCA2365 will overheat very rapidly when oscillating at very high frequencies, so any debugging of stability problems should be done very rapidly, and for short periods only! Specifically, it is good practice to take the 0V connection to the feedback resistor, input resistors, input decoupling, etc, as appropriate, to the power supply as a separate connection from the load, Zobel network, etc, to isolate the input as far as possible from the output. In all cases, each power op-amp should have



TCA365 (Single On-Amn) TCA3365 (Dual On-Amn)

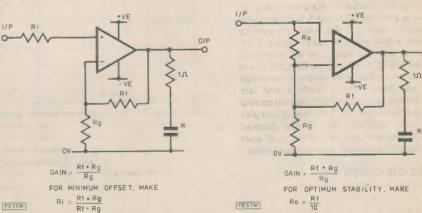


Fig. 3c. Non-inverting, high gain

Fig. 3d. Non-inverting, low gain

Fig. 3. Basic power op-amp circuits

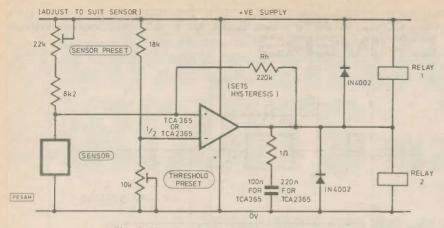


Fig. 4. Simple sensor detector and switch

100µF capacitors between its supply rails and 0 volts, or simply across its rails in the case of single supply systems.

When inductive loads are to be driven, diodes should be connected between the opamp output and the supply rails, as shown in Figs. 4, 6 and 8. This protects the op-amp's driver transistors from the huge back e.m.f. spikes generated when inductive loads are suddenly turned off.

APPLICATIONS

The uses for these i.c.s fall mostly into the realms of control and switching. They will amplify and drive audio signals, but not with the fidelity that can be achieved by audio power amplifiers specifically designed for the task. Essentially, these i.c.s are excellent for use on many occasions when an ordinary opamp simply runs out of drive capability. Some examples of switching applications are shown in Figs. 4, 5 and 6.

A simple sensor circuit is shown in Fig. 4 using the power op-amp as a comparator and directly driving relays 1 and 2. The sensor can be any device which varies in resistance in

proportion to a required effect. For example, a light dependent resistor (e.g. ORP12) or thermistor would allow the sensing of light level or temperature respectively. The sensor preset scales the voltage range produced by the sensor at the op-amps non-inverting input, while the threshold preset alters the level at which the op-amp changes state. Rh provides some hysteresis to stop the op-amp 'hunting' or 'chattering' when the sensed value is just on the threshold point.

A square wave oscillator is formed by the power op-amp in Fig. 5. The mark/space ratio potentiometer adjusts the charge and discharge paths for C_T such that their sum is always constant (i.e. the frequency does not vary) but the mark/space ratio can be adjusted over a wide range. The frequency itself is set by a combination of the value of C_T and the setting of the 100k 'frequency' potentiometer. This circuit is capable, by virtue of the power op-amp, of driving pulses of several

amps into any suitable load. Output diodes should be added, as shown in the other circuits, if the load is to be an inductive one.

DIFFERENTIAL DRIVING

Finally, Fig. 6 shows two power op-amps driving a d.c. motor in a 'bridge', or differential drive mode. This allows the direction of rotation of the motor to be changed. IC1 and IC2 are arranged as comparators with RH and RL setting the threshold voltage VT, and are designed to be driven by logic signals A and B. If both inputs A and B are at a low level (logic 0), both sides of the motor will be at a low level (0V). If both inputs are high (logic 1), then both sides of the motor will be at a high level, near to the +ve supply rail. In both these cases the motor will not run, since there is no differential voltage across it—both terminals of the motor are at the same voltage. However, if one input is high, and the other low, the motor will run in one direction or the other. Normally, VT should be set to a suitable level for the logic family which is used to control IC1 and IC2; ideally, RH and RL should be taken from the logic's power supplies, not the +ve power supply as shown, to ensure accuracy of the threshold voltage.

The TCA365 and TCA2365 are ideal for use in controlling motors, relays, magnetic valves, and solenoids. They can also make a good basis for the design of regulated power supplies. Their current limiting makes them especially suitable for driving filament lamps and other unusual loads, and their op-amp configuration makes for easy interfacing of these loads with both analogue and digital circuitry. When stability is taken into consideration these are easy and effective to use, and provide an economic solution to many power driving problems. Both i.c.s are available from Electrovalue, 28 St. Jude's Road, Englefield Green, Egham, Surrey.

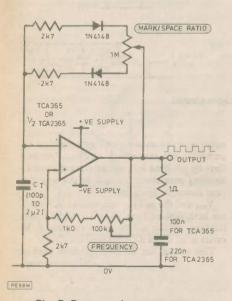


Fig. 5. Power pulse generator

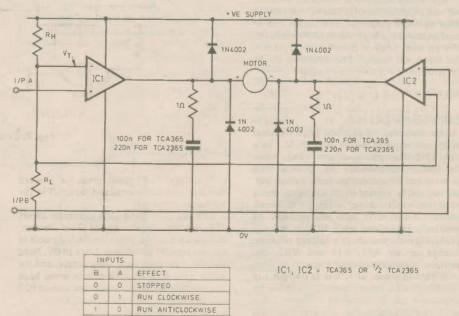


Fig. 6. Bi-directional motor control

STOPPED

MICROPROCESSOR CONTROLLED DC MOTOR DRIVERS

LAST month we looked at a timer circuit triggered by a microprocessor. This month we have another microprocessor based project, to allow the analogue driving of d.c. motors. Again, the circuit assumes the use of the Z80 microprocessor, although it is very easily adaptable for other devices. The circuitry is shown in Figs. 7 and 8 and the Veroboard layout in Fig. 9. The circuit consists of two separate sections; the decode, and the driver. Up to 8 drivers can be operated by one common decoder.

The address decoding is done in a similar way to last month's project. IC1 compares the most significant nibble (4 bits) of the 8 bit port address with the settings of S1 to S4. Each switch is turned off to correspond to a logic 1, and on for a logic 0. The comparison is only enabled when both IORQ and WR are at logic 0 (determined by IC5c), corresponding to the microprocessor performing an I/O write instruction. IC2 is a 3-to-8 line decoder used for the least significant nibble of the port address. Address line A3 must be held at logic 0 and the other 3 lines then provide the address of the driver circuit required. The least significant nibble of the driver address will therefore be Ø to 7, as determined by the latch output of IC2 used. The outputs of IC2 are inverted, and are wired to the LATCH inputs of any required driver circuits. Hence, if one particular driver circuit LATCH input was connected to LATCH output 3 of IC2, switch S1 was off and switches S2 to S4 were all on, that driver circuit would respond to address 13H (i.e. 19 in decimal). Driver circuits can thus be provided at port addresses 00H to 07H, 10H to 17H, 20H to 27H, 30 to 37H, etc.

IC3, with associated components, provides a 5 volt regulated supply. This can be omitted if the microcomputer's own 5V supply is to be used to power the logic supply to the circuitry. IC4 provides a reference voltage which tracks the Vp power supply. This reference will be approximately 1.8V for a 12V supply.

THE DRIVER CIRCUITRY

IC6 is a digital to analogue (D/A) converter with a built-in data latch, which connects to the microprocessor's data bus. Data is latched in by the required output of IC2. IC7 is a TCA2365 dual power op-amp which drives the motor differentially to provide both forward and reverse control from a single supply voltage. (It's based on an analogue version of the differential driver in Fig. 6). IC7a amplifies the output of IC6 and provides the positive output phase, while IC7b inverts this positive drive signal about a half-rail reference voltage set by R17, R18 and VR2, and provides the negative output phase.

When the output of IC6 is at 0V, pin 1 of IC7a is near to 0V and pin 9 of IC7b is near to the +ve supply. When the output of IC6 is at V_{ref}, the reverse is true. When IC6's output is at half V_{ref}, both power op-amp outputs are at half the supply rail and the motor is stationary. Presets VR1 and VR2 aiter the gain and offset of the output voltages, and D1,

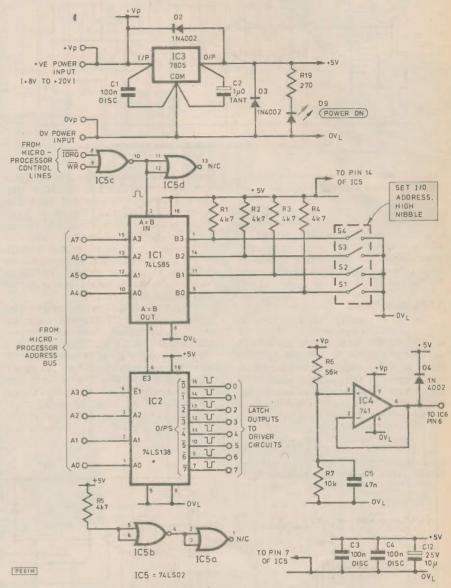


Fig. 7. Decoder circuit

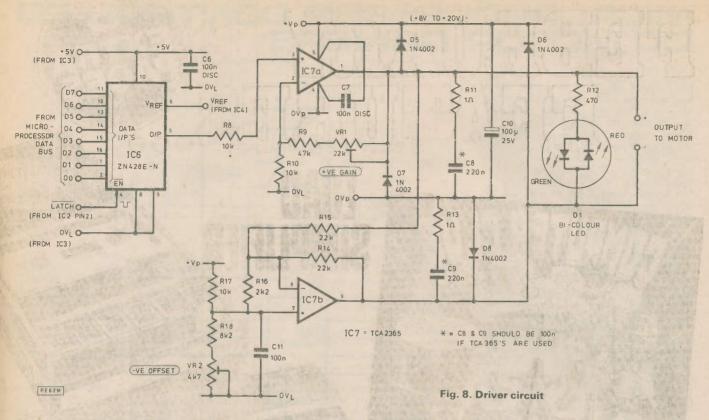
a 'Bi-Colour' l.e.d., glows green for forward direction, red for reverse and turns off in the stationary condition.

The use of an 8 bit D/A converter allows 127 forward speeds and 127 in reverse, although it is unlikely that the electric motor in use will operate all the way down to 0V. Note that 0V_L, the logic zero volts supply, and the power zero volts 0V_P, have been wired back separately to the power input area around IC3 to help ensure stability and an absence of noise problems with the logic supplies. GREAT CARE must be taken when wiring up the circuitry and assembling components on the Veroboard, and tests should be done prior to connecting to the computer as far as

possible. I can assure you, from practical experience, that connecting +12V to the data lines by accident will certainly cause some interesting permanent changes to the way that your computer operates!

V_{ref}, and the half rail reference to IC7 pin 7, are both derived from the +V_P rail to ensure tracking of the motor drive outputs if V_P varies at all under different load conditions.

This circuit has successfully been used to control a 12 volt model train set by microcomputer. The only programming requirement is to output the relevant motor speed values to the port or ports in question. Hence, for a port address of 24 (Hex) for example, the assembled Z80 machine code for full speed forwards



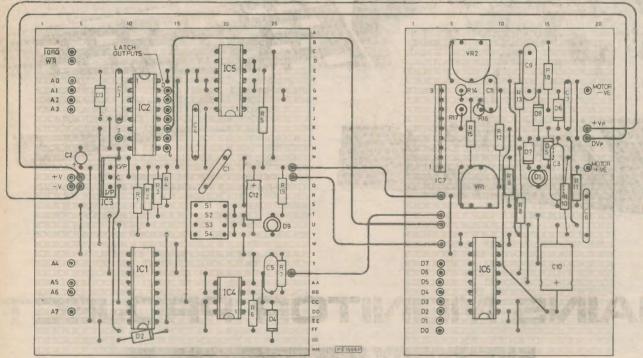


Fig. 9. Veroboard layout

could look like this:

3E ØØ LD A,ØFFH

; Put required value in Accumulator.

D3 24 OUT (24H),A

; Output the Accumulator to the port.

In BASIC, the simple instruction OUT 36,

255 would suffice. (36 is the decimal equivalent of 24H, the port address, and 255 the decimal equivalent of ØFFH.) For full speed reverse use the value ØØH (Ø decimal), for stopped use Ø7FH (127 decimal), and for slower speeds use values in between. Finally,

don't forget the heatsink on IC7! The i.c. has been placed at the edge of the board to allow for this. The resulting motor speed control provides a simple illustration of a typical use for power op-amps, either as two single devices or a pair as used specifically in Fig. 9.

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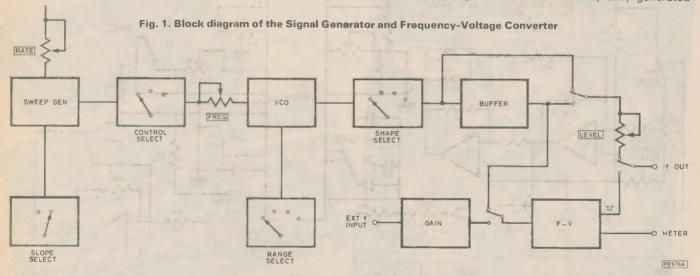
Signal Generator 2.F-V Converter

JOHN M. H. BECKER

A NY electronics enthusiast needs a signal generator and frequency meter nearly as much as a soldering iron and multimeter. The last two should be part of anyone's workshop but the degree of enthusiasm does not necessarily warrant the expense of highly accurate generators and counters. Often only an indication of approximate frequencies is required, together with a unit that makes readily controllable sounds with suitably shaped waveforms.

GENERATOR CHIP

An XR2206 function generator chip has been chosen in preferance to the normally selected type 8038 as it has a greater variety of waveforms available, together with a wider sweep range on each selected setting. The oscillograms show the wide range of waveforms available. The basic frequency range is selected by S1, bringing in the desired frequency setting capacitor C4–C7. The frequency generated



This unit has been designed as a reasonable quality, moderate cost, dual purpose unit suitable for average and addicted constructors alike. It produces well shaped waveforms of frequencies ranging from 2Hz to 78kHz in four tunable ranges, and includes automatic ramp control of a frequency sweep, both upwards and downwards. Additionally it includes a frequency to voltage converter that can be coupled to an ordinary multimeter, or digital voltmeter to give a direct read out of the approximate frequency being generated, or fed in from an external source. It is intended for use with an existing power supply or, for short periods with batteries, from 9V up to 18V dc. Provision has also been made to mount discrete power supply components directly onto the p.c.b. so that the unit can be fully independent of other equipment.

can then be controlled by either a varying voltage or a varying current. For normal manual selection of the desired frequency, current control is used, and is relative to the resistance of the total of VR4, VR5 and R8. In this mode VR5 is taken directly to ground by S5. As the resistance of these potentiometers decreases, so the output frequency rises in relation to the formula: $f = 1/(R \times (C/1000)) \times 1000$, where C is the value of the selected capacitor C4 to C7 in microfarads, and R is the total resistance in circuit with pin 8 of IC2.

VR4 provides coarse tuning of the frequency, and VR5 fine tuning. The maximum resistance range that is permissible with IC2 is from 1K to 2M, though is limited to a maximum of about 1M in this unit. This allows a reasonable overlap between the switched ranges, without making the

Photograph illustrating the external assembly of the Signal Generator and F-V Converter



SPECIFICATION...

TOLERANCE

The figures quoted refer to those obtained on the prototype and may vary slightly in other units in accordance with normal component tolerance factors.

FREQUENCY TO VOLTAGE CONVERTER

Good linearity from 200Hz to 30kHz directly readable on a standard multimeter or digital voltmeter. Accessible internally and externally.

FREQUENCY GENERATOR

Basic switched frequency ranges = (1) 2Hz to 81Hz, (2) 20Hz to 851Hz, (3) 200Hz to 8400Hz, (4) 1970Hz to 78800Hz. Coarse and fine tuning of selected frequency range. Switch selected waveforms—sine, triangle, square, ramp, pulse, and variations (see photographs 1–6). Sweep modulator—rising and falling ramps, switch selectable, rate 6 to 40 cycles per minute. Frequency outputs—switched, buffered or unbuffered via amplitude control from nil to 5V peak to peak. Fixed 0V/+5V amplitude square wave derived from internal oscillator or external source up to about 80kHz. Four switched reference frequencies.

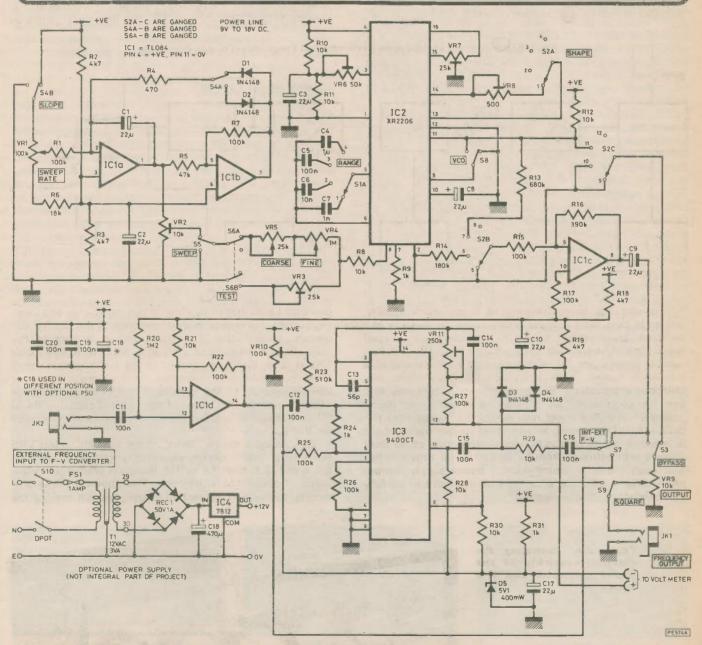


Fig. 2. Complete circuit diagram of the Signal Generator and Frequency-Voltage Converter

fine tuning too coarse. Switching in VR3 by S6 instead of VR4 and 5, a preset reference frequency can be selected. The i.c. contains its own current controlled amplifier and the amplitude of the signal generated as seen at pin 2, is presettable by VR6. This controls the sine, triangle, and ramp waveform maximum levels. The squarewave however is derived from a different section and is at approximately full line level amplitude as determined by the current through the load resistor R12. The shape of the triangle and ramp waveforms is predetermined within IC2 itself. For sine wave related waveforms, shaping is preset by VR8, and the symmetry trimmed by VR7.

WAVEFORM SELECTION

Three basic waveform selections can be chosen with S2. With S8 open, the choice is sine, triangle and square. In position 1 (sinewave) the output comes from pin 2 of IC2, and VR8 is in circuit, controlling the sine shape. In position 2. (triangle wave), the output again is from pin 2, but at a level approximately twice that of the sine wave and VR8 is out of circuit. In position three (squarewave), the output is taken from pin 11 IC2. With S8 closed the squarewave is directly fed to the control pin 9, and internal circuitry of the chip is automatically switched by it to produce ramp related waveforms in the first two positions of S2. In this mode the frequency of oscillation now becomes affected by the value of R9 and the formula changes to: $f = (2/C/1000) \times (1/R) \times$ 1000, using the same parameters as before. Effectively this means that the frequency with S8 closed will be approximately twice that with it open. In position S2, looking at the inverted output of IC1C, the rising ramp is sine shaped, followed by the steep drop. In position 2 the rising ramp is linear, again followed by a steep drop. Study of the second formula though will show that the steepness of the drop is related to values of R9, and the controlling resistance on pin 8. As the two resistances approach equality, so the steepness lessens, and a falling ramp also develops. The best ramps are thus created with the resistance on pin 8 at the greater end of the scale. In position 3 the output is again from pin 11, but consists of a mark-space pulse, the duty cycle of which determined by the formula: RA/(RA + RB), where RA is the resistance on pin 7, and RB that on pin 8. The negative going pulse length is moderately constant throughout the range for the same capacitance selection. The mark-space factor is also reflected in the shape of the ramps with a flattening of the apex, but is really only noticeable at small values of capacitance.

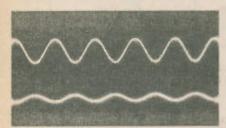
OUTPUT ROUTING

In most instances it is preferable for the amplitude of the different waveforms seen at the final output to be roughly equal. As previously seen there is an inherent level difference between the three main waveform ranges, IC1C is thus included to even these out. The gain of this stage is of course dependent upon the relationship of the total input resistance to the value of the feedback resistor R16. The choice of resistors R13–R15 ensures a reasonable match of the levels. The inverted phase output from IC1C is decoupled by C9, taken via S3 to the level control VR9 and then to the output via S9. However the frequency pass range of IC1C is less than that of the range available from IC2. For normal audio applications, the frequency response of IC1C is sufficiently adequate, but distortion becomes more prevalent as the frequency rises above about 30kHz, as shown in the oscillograms.

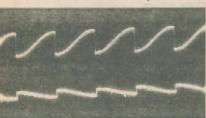
Additionally the loading of C9 causes square wave distortion at lower frequencies. S3 is thus included to bypass IC1C so that the output is unbuffered allowing the full range of IC2 to be used. Note though that the unbuffered output also contains a d.c. bias that is approximately half line level with S2 in positions 1 & 2, and that the phase is inverted.

SWEEP OSCILLATOR

When testing out some circuits it is sometimes preferable for the frequency range to be swept upward or downwards at a controlled automatic rate rather than by manual control of a potentiometer. The ramp generating circuit around IC1A & IC1B provides this control. The frequency range of ramp generation is determined by C1 with larger values giving slower rates. VR1 provides the tuning of the sweep rate setting. The direction of the ramp produced is governed by the direction of voltage flow through D1 and D2. S4 selects the diode routing, and reverses the polarity of the controlling voltage through VR1 in relation to the reference level at C2. The changing d.c. voltage produced by the ramp controls IC2 via VR2, S9, VR4 and VR5. In this mode voltage control of IC2 is being employed in addition to current control. For correct operation of IC2 the voltage sweep seen at the wiper of VR2 must lie below 3V, above this and the oscillator of IC2 will cease. VR2 thus needs adjustment to keep the sweep voltage within this range. The frequency control range provided by the varying voltage is less than that produced in the manual mode, and VR4 and VR5 are used to select the desired band width.



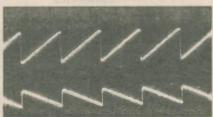
Sine (normal) S2,



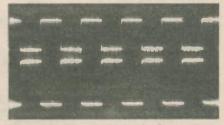
Sine (ramp) S2₁



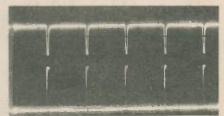
Triangle (normal) S2₂



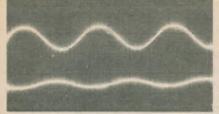
Triangle (ramp) S2₂



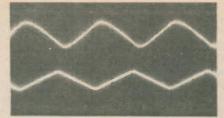
Square (normal) S23



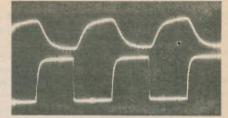
Square (pulse) S2₃







Triangle (high freq) S22



Ramp (high freq) \$23

FREQUENCY TO VOLTAGE CONVERTER

IC3 performs the f-to-v conversion, producing an output voltage that, within the range, is related linearly to the frequency fed in. The range available is determined by the gain given to the feedback via R27 and VR11, with a slew rate and ripple reduction level set by C14. High values for C14 will give reduced ripple for lower frequency signals, but will increase the time taken for the voltage to stabilise when the frequency is changed. The relative minimum output voltage in the absence of an input frequency should be as close to zero as can be set by the bias control VR10, VR11 is used to set the maximum range. The output voltage is referenced to an intermediate level of about 5V as set by Zener diode D5. The negative lead of the meter used to monitor the voltage is taken to this level, and the positive lead to the output from pin 12, IC3. If the meter negative lead were to be taken to the normal OV or ground line then the reading would also contain the reference voltage of 5V and inaccurate readings would result. For stable operation of the conversion, the input frequency seen at pin 11, IC3 should be at a constant level of about 1V p-p. To maintain this amplitude even for low level input signals, the signals are taken via the gain stage IC1D for external signals which gives an amplification of about, a little over 100. The signal is then attenuated to the optimum level by diodes D3 & D4. For internal frequency reading, the signal is taken direct from the output of IC1C, and similarly attenuated. S7 selects the choice of internal or external frequency monitoring. In addition to producing a frequency related voltage, IC3 also produces a square wave output of 5V amplitude. There is a slight time lag between the edges of the input frequency and of the out-

put 5V squarewave. S9 can switch in this frequency output in place of that produced directly by IC2. This means that an external frequency of indifferent level and shape can be converted for controlling circuits that require a 5 volt squarewave. The external loading permissible though is limited by the value of R30 and too great a load will reduce the voltage.

POWER SUPPLY

56p polystyrene

470u 25V elect

100k skeleton

250k skeleton

Most enthusiasts probably already have power supplies in their workshop capable of driving this unit, and so a separate one is not included. The minimum voltage requirement is 9V, and the maximum permissible +18V as dictated by the limits of IC3. The current drawn is about 30mA, up to 20mA of which is consumed by IC2. This current is a bit too high for the unit to be powered for long periods from a battery supply, though one could be used briefly in an emergency. Alternatively a battery eliminator might be suitable, providing it can tolerate the current without the voltage dropping below 9V and that the ripple content is negligible. The printed circuit board though includes positions for the mounting of the rectifier and voltage regulator as shown in the suggested optional 12V power supply circuit. This supply was not used in the prototype and is not regarded as an integral part of the project. The transformer should be bolted to the metal box. and normal mains electricity safety precautions observed. Note that with this suggested power supply C18 has its positive end connected to a different track position, and it may be necessary to mount it vertically rather than horizontally. The use of a heat sink with the regulator i.c. should not be necessary.

COMPONENTS . . .

RESISTORS

R1,R7,R15,R17,R22,				,, op, 20, 0,00t.
R25-R27	100k (8 off)			
R2,R3,R18,R19	4k7 (4 off)			
R4	470	SEMICO	NDUCT	ORS
R5	47k	IC1	Т	1004 (avad as assa)
R6	18k	IC2		L084 (quad op-amp) (R2206
R8,R10,R11,R12,R21		IC3		
R28-R30	10k (8 off)	D1-D4		9400CT (R.S. 307 070) N4148 (4 off)
R9.R24.R31	1k (3 off)	D5		
R13	680k	DS	2	5V1 Zener, 400mW
R14	180k			
R16	390k	D	OTENT	OMETERS
R20	1M2		OIEIVII	OMETERS
R23	510k		VR1	100k mono rota
All resistors ½W ±5%			VR2	10k skeleton
			VR3,VR7	
CAPACITORS			VR4	1M mono rota
C1-C3,C8-C10,C17	22µ, 10V elect.	(7 off)	VR5	25k mono rota
C4	1μ, 63V elect.		VR6	50k skeleton
C5,C11,C12,C14C16,			VR8	500 skeleton
C19,C20	100n polyester	(8 off)	VR9	10k mono rota

10n polystyrene

1n polystyrene

VR10

VR11

C13

C18

MISCELLANEOUS

P.c.b. and p.c.b. clips (4 off) Round knobs (6 off) I.c. sockets, 16 pin, 14 pin (2 off) Jack socket, 3.5mm Jack sockets mono (2 off) Box and rubber feet Meter terminals (2 off)

SWITCHES

S1,S2	3P4W (2 off
S3,S5,S7-S9	SPDT (5 off)
S 4,S6	DPDT (2 off)

Constructor's Note

A complete kit of parts is available from: Phonosonics, 8 Finucane Drive, Orpington, Kent BR5 4ED. Price £54.00. inclusive of VAT. Post and packing £1.00.

C6

ASSEMBLY

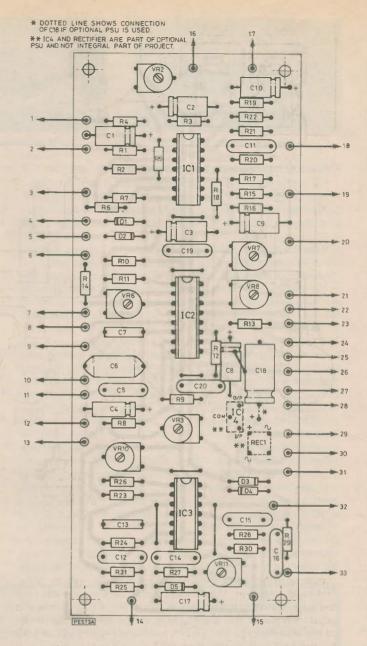
After the straight forward component assembly and subsequent joint checking procedure has been carried out, wiring should be commenced in a methodical fashion, ticking off each wire on the wiring diagram as connections are made. First connect up all the panel controls between themselves. Secondly wire up to all the p.c.b. points closest to the front panel. Finally connect up the rear and remaining connection points. These latter wires should preferably be brought under or round the edges of the p.c.b. Taking them over makes the wiring untidy. Keep the wiring short, but long enough for turning the board over for examination without over straining the connections (too much flexing of taut wires can cause breaking at the joins). The prototype has the meter terminals on the front, but with hindsight, mounting them on the back would be better.

The regulator IC4, and the rectifier REC1, are part of the optional power supply, together with the transformer T1. These components may be omitted if not required as the unit will run quite efficiently from any 9V battery.

SETTING UP

A fair selection of presets has been included to enable the maximum accuracy to be obtained throughout the unit. The only really critical one is VR2, as the sweep control may not operate if this is incorrectly set. Inadequate setting of the others will only cause lack of linearity. If an oscilloscope is not available intelligent decisions will need to be made, listening to the sounds while adjusting the presets.

First, S1 position 1 (lowest freq), S2 position 1 (sine), S3 on (buffered output), S4 either way, S5 off (sweep off), S6 off (manual freq control), S7 off (internal f-v), S8 off (standard waveforms), S9 off (vco output), VR1–3 midway, VR4–5 max clockwise (highest freq), VR6–8 midway, VR9 max, VR10–11 midway. Switch on and check that pin 3 IC1A, pin 3 IC2 are at approximately half line voltage, and that the positive end of D5 is at about 5V. Plug in to normal amplifier. If no sound is heard then check the wiring, and that the switches are wired the correct way up. Assuming that sound is heard, check that VR4 and 5 vary the frequency, and that S1 changes the ranges. Switch on S6, and adjust VR3 to the desired fixed frequency on the second range of S1. In the author's unit this was set for approximately 440Hz. Check that S8 brings in the ramp associated



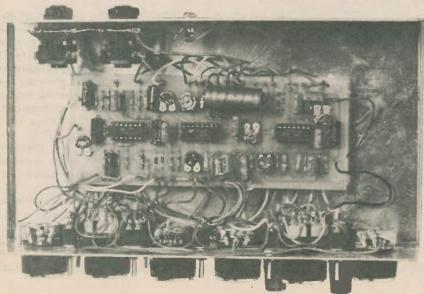


Fig. 3. (Above) Showing the p.c.b. design and component layout of the Signal Generator. (Left) Photograph illustrating the internal view of the chassis assembly showing the switch, sockets and p.c.b. layout

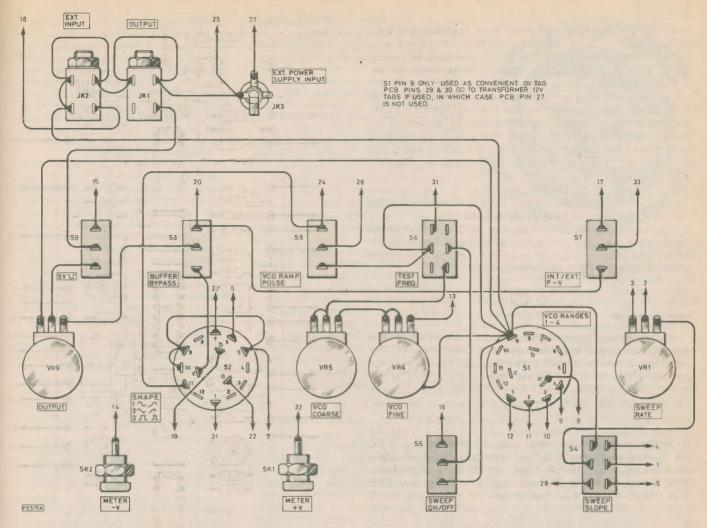


Fig. 4. Wiring diagram of the Signal Generator

ranges of waveforms, then switch back to the normal range, and to squarewave. Monitor the output jack socket and note the squarewave amplitude level. Switch to triangle wave and adjust VR6 until the amplitude is similar without flattening of the waveform peaks. Switch to sine wave and adjust VR8 for the best sine shape, then VR7 for the best symmetry. If necessary readjust VR8.

Switch S3 to bypass and check all waveforms can be switched in, though as previously stated they will be at widely varying levels. Switch S6 back to manual control, then S5 to sweep control. Check that a ramp waveform appears at pin 1 IC1A, and that switching S4 varies the direction, also that VR1 varies the rate with the ramp in both directions. Return scope probe to the output jack socket, and adjust VR2 for the smoothest sweep response. If the wiper is too far to the OV end the generator frequency will dwell at the high end, with it too far towards IC1 the generator will cut out at the low frequency end. With careful adjustment a smoothly varying rising or falling sweep range can be set. Switch off the sweep control and set a frequency output from IC2 of precisely 10kHz. Check that an attenuated version of this frequency reaches pin 11 IC3 via S7. With the external input jack socket grounded (as it will be without a jack plug in), switch S7 to external. Connect a multimeter across the meter output terminals and adjust VR10 for a reading of exactly zero volts. Start off with a meter range of

about 5 volts, then after the initial adjustment has been made the meter can be switched to its lowest range for greater precision. Set meter to a range for monitoring exactly 1V. Switch S7 back so that the 10kHz signal reaches IC3. Very carefully adjust VR11 until a precise voltage of 1 volt is obtained.

The maximum frequency that can be read will be about 30kHz to 35kHz, beyond this IC3 will fail to respond and show a constant reading of around 3.5V. Applying a 1kHz signal should produce approximately 0.1V. Tracking downwards in frequency, linearity will be roughly maintained until about 200 Hz or so, depending on the accuracy of the setting of VR10 and VR11. Once the boundary extremes have been established, a direct reading of frequency can be taken from the multimeter by converting the voltage into the readily calculable frequency. Thus if 1V = 10kHz, 3V = 30kHz, 0.5V = 5kHz, 0.05V = 500Hz, etc. Check that an external frequency can be monitored in the same way, then finally that a squarewave output of about 5V is available from pin 8 to IC2.

After setting up the f-v converter the frequency controls of the unit can be calibrated and control legends applied to the panel, using a rub down lettering like letraset or similar, then coating them with a suitable spray protector. If care has been taken in the setting up, the end result will be a marvellously versatile dual purpose new unit for the workshop.



Perhaps the most interesting development during the past few months has been the visual detection of the ring-system surrounding Uranus. The rings were first found indirectly, because they produced a series of occultations of a faint star; subsequently, D. A. Allen and J. Crawford, at Siding Spring Observatory in Australia, photographed them in infra-red.

Studies of them have now been carried out by Richard Terrile and Bradford Smith, using the 2.5-metre reflector at the Las Campanas Observatory in Chile together with a highly sensitive CCD or Charge-Coupled Device. The ring-system is clearly shown, together with all five known satellites-Miranda, Ariel, Umbriel, Titania and Oberon. The pictures show the great power of the CCD, which is at least thirty times more sensitive than any photographic plate.

The rings of Uranus are quite unlike those of Saturn. Terrile and Smith find that their albedo or reflecting power is only about 2 per cent, so that they are blacker than coal-dust. They are also narrow; there are at least eight rings, not all of which are perfectly circular, and their composition is unknown!

If all goes well, we should learn more about them in January 1986, when the Voyager 2 spacecraft makes its pass of Uranus, Meanwhile, there is speculation about the possibility of a ring-system round the outermost giant, Neptune, but the presence there of a large retrograde satellite (Triton) may have prevented any rings from being formed. Again, we pin our hopes on Voyager 2, which will rendezvous with Neptune in the late summer of 1989.

HALLEY'S COMET

Halley's Comet is, of course, still much too faint to be detected except with very powerful instruments, but recent studies show that it may prove to be somewhat brighter than had been expected. Unfortunately, this does not mean that it will be a brilliant spectacle, as it has been on many past returns.

It should become a naked-eye object at the end of 1985, before perihelion passage on 9 February, 1986, but British observers will need clear skies. When at its best, after perihelion, the comet will be in the far southwell placed for Australians and South Africans, but not for Europeans, who will not see it at all until it has faded considerably.

NOVA CYGNI—A NEW LOOK

On the evening of 29 August, 1975, I went into my observatory to make some routine observations of variable stars. When I looked up at the familiar constellation of Cygnus, I had a surprise. There, shining down unmistakably, was a bright star which had certainly not been there on the previous night. I estimated its magnitude as 2.4, slightly fainter than Gamma Cygni, the central star of the "cross" of Cygnus.

Having satisfied myself that it really was a new star or nova, I made a telephone call to the observatory at Herstmonceux. I was, of course, fairly sure that the star had already been reported—and so it proved; it had been discovered some hours earlier by Kentaro Osada in Japan, before darkness fell over England. I imagine that I was about sixtieth in the list of independent discoverers; the star could not possibly have been overlooked by anyone with more than a rudimentary knowledge of the constellations.

The most remarkable fact about Nova Cygni was that it brightened up by at least nineteen magnitudes in only a'few hours. This was a record, both for amplitude and for speed. Its decline was also unusually quick, I estimated its magnitude as 1.8 on 30 August, so that it was then much the brightest star in the constellation apart from Deneb; but it had dropped to below 3 by 1 September, below 5 by 4 September, and faded below naked-eye visibility by 7 September, when I saw it as fiery red-in fact, as red as any star I have ever seen. Within a few months it had become too faint to be observed except with powerful telescopes.

Apart from Nova Cygni, only three novae seen since 1930 have attained the first magnitude: DQ Herculis (1934), CP Lacertae (1936) and CP Puppis (1942), though others have become visible with the naked eyenotably HR Delphini, which was discovered in 1967 by the well-known English amateur George Alcock and had a very prolonged maximum of around the fourth magnitude. It is still above magnitude 13, and probably will not fade much further, as this was also its preoutburst magnitude.

However, the exceptional behaviour of Nova Cygni has led to particularly detailed studies of it, and efforts have been made to detect a cloud of débris round it. This has now been a successful operation.

THE SKY THIS MONTH

Winter skies are always glorious, thanks to the presence of Orion, the Hunter, and his magnificent retinue, but at the moment the dearth of bright planets continues-apart from Venus, which is at its very best in the evenings. Mercury is, in theory, a morning object, and may indeed be glimpsed just before sunrise, but it is well south of the celestial equator, so that European observers are unfavourably placed.

Mars may be seen in the south-west during the early evening, and moves from Aquarius into Pisces by the end of the month, but its magnitude is now only 1-2, and no telescope will show much upon its surface. Saturn, in Libra, rises well before the Sun, but is low down and by no means prominent, while Jupiter passes through conjunction on 14 January and is therefore out of view altogether. There are no eclipses this month, and no bright comets are expected. The Moon is full on 7 January, and new on the 21st.

During winter evenings the brilliant yellow star Capella is almost overhead (a position occupied by the equally brilliant Vega during evenings in summer). Close beside Capella lie the three fainter stars making up a triangle. They have been nicknamed the Haedi or 'Kids', and two of them are very remarkable objects.

Epsilon Aurigae, at the apex of the triangle, is an extremely luminous supergiant, at least 60,000 times as powerful as the Sun. Every 27 years it fades down by almost a magnitude, not because it is intrinsically variable but because it is being eclipsed by a companion which has never been seen at all.

The nature of the invisible secondary is still a matter for debate. It was once believed to be a very young star, not yet hot enough to shine; there were also suggestions that it might be a black hole, but it now seems more likely that it is a relatively small, hot star with an associated extensive shell of material. The last eclipse ended in 1984, so that for more than two decades nothing further will be happening.

Look at the 'Kids' and you will see that Epsilon is now the brightest member of the trio. The faintest, Sadatoni or Zeta Aurigae, is also an eclipsing binary with a period of 972 days, but we know much more about it; the primary is a red supergiant, while the secondary is a much smaller and hotter star.

It is sheer coincidence that these two exceptional eclipsing binaries lie side by side in the sky. There is no true connection between them; Epsilon is much further away from us than Zeta.

Using the 82-inch reflector at the McDonald observatory in Texas, G. and A. de Vaucouleurs have recorded the débris unmistakably. The cloud shows up as an elliptical blur, 3.5×2.5 seconds of arc across, with an integrated magnitude of about $16\frac{1}{2}$. Presumably it is expanding; and if the distance of the nova is 4,500 light-years, as seems likely, the expansion rate is approximately 800 miles per second.

BINARY SYSTEM

According to modern theory, a nova is a binary system, made up of an ordinary main sequence star together with a white dwarf. White dwarfs are stars far advanced in their evolution; they have used up their nuclear "fuel", and have become very small and almost incredibly dense.

In a nova, the white dwarf pulls material away from its larger, less dense companion, and there is a build-up of material around the dwarf, leading eventually to instability and a violent, usually short-lived outburst. Associated debris is only to be expected, and has been detected with many former novae—such as Nova Persei 1901 and Nova Aquilae

1918, both of which became much more brilliant than Nova Cygni. Indeed, for a brief period Nova Aquilae outshone every star in the sky with the exception of Sirius.

SUPERNOVAE

There is a fundamental difference between ordinary novae and the much more powerful supernovae, which are much less common. Only four supernovae have been seen in our Galaxy during the past thousand years; those of 1006, 1054, 1572 and 1604—all before the invention of the telescope, though supernovae are so luminous that they may be detected in external galaxies many millions of light-years away.

From the few accounts which have come down to us, the 1006 supernovae, in the southern constellation of Lupus, became as bright as the quarter-moon, while the other three outshone Venus. The 1054 supernova has left the gas-cloud of the Crab Nebula, which contains a pulsar.

For many years the Crab was regarded as unique, but recently a very similar supernova remnant, including a pulsar, has been found in the Large Cloud of Magellan, more than

150,000 light-years from us. Pulsars are rapidly-spinning neutron stars which slow down as they age. From the measured slowing-down of the Large Cloud pulsar, it has been estimated that the outburst occurred about a thousand years before our present-day view of it.

The rapid increase of Nova Cygni 1975 raised initial hopes that it might be a supernova—something which astronomers would warmly welcome, because it cannot be said that our knowledge of supernova mechanism is at all reliable (there seem, indeed, to be two quite different types of supernovae, one of which involves the collapse of a massive star while the other indicates the complete destruction of a white dwarf).

We could learn much more if we had the opportunity to study a relatively nearby supernova with modern equipment. Nova Cygni was therefore something of a disappointment; but it is still extremely interesting, and it will be important to find out how the newly-discovered cloud of debris develops.

There is one rather sobering thought. When we look out into the Galaxy, we are also looking into the past. Nova Cygni exploded well over four thousand years ago; the expanding cloud we see today was produced long before astronomy had become a true science!

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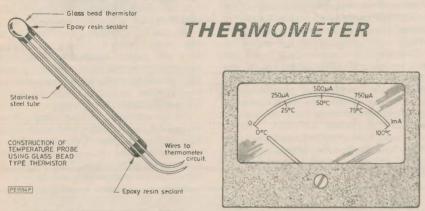
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THERMISTOR



CALIBRATION OF METER 1mA FS.D.

Construction and calibration of the Thermistor Thermometer

RT	R1	R2	R5	R6	R7
JA -03	7k5	5k6	22k	1k2	0.C.
VA3704	10 k	6k2	10k	1k	10 k
TABLE 1					

OC.	0	30	70	100
ERROR	+3.3	-2·0 -2·5	+1.7	-2·6 -3·2
TABLE 2		ىك	+	1

HE conventional bridge circuit recommended for thermistors is somewhat inaccurate. Better results can be obtained using the arrangement shown here. The op.amp, IC2 acts as a voltage source, with current measured by the meter ME1. This configuration corrects for most of the thermistor's non-linearity. An offset current flows through R5 and VR1, and sensitivity is set by VR2 and R6. Assuming a fullscale current of 1mA, an output of 1mV/°C is conveniently obtained at the output and this can be used to drive a chart recorder, for example. The supply voltage is regulated by IC1, and a 3-way switch allows the battery to be checked. Resistor values for two types of NTC thermistor are given in Table 1. JA-03 is metal-sheathed (RS no. 151-120) and VA3704 (Mullard no. 2322-627-11472) is a glass-bead device. Both have a resistance at 50°C, of the order of 1k7.

Kettles and ice-buckets are unpredictable gadgets! Calibration was done at 10, 50 and 90°C, using a water-bath and laboratory-grade mercury thermometer. The error curve is cubic, with a deviation within 2 or 3 degrees centigrade over most of the range, increasing near the 0° and 100°C limits.

100°C limits. C. J. D. Catto, Elsworth, Cambridge. TC1 78 L05 1mV/°C R1 OUTPUT ** See text ME1 1mA F.S (70 OHM) C 4 R3 IC2 LM312 100 500 51 Positions OFF BATT, CHECK 0°C R2 * C1 100 n PETOM

LOGIC RECORDER

THE logic recorder is designed to fill the gap between the logic probe and the logic analyser by displaying a sequence of eight data bits on a bank of l.e.d.s. Data is stored synchronously with the system clock after a trigger pulse from the circuit under test.

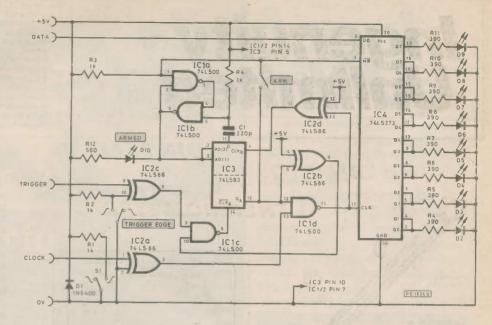
Data is fed into IC4, an octal D-type flip-flop wired as a shift register, though a 74LS164 shift register could be used instead. D2 represents the most recent data.

Suppose that latch IC la/b is set so that D10 is unlit. IC1 pin 6 is high so IC3 is reset, its 'A' output is low, IC1d is disabled and IC1c is enabled via IC2b. When the ARM button is pressed the latch sets, lighting D10 and freeing IC3 to count. On the rising edge of IC2c pin 8, the single-bit counter in IC3 clocks, disabling IC1c and the ARM button and enabling IC1d to clock IC4 and, via IC2d, the 3-bit section of IC3.

After eight clock pulses from the system under test, IC3 pin 11 goes low, resetting the latch via C1. Provided that the ARM button has been released the logic recorder resets and displays the data received until it is rearmed.

IC2a and IC2c are used as programmable inverters to select the desired trigger and clock edges. DI protects the recorder against reverse polarity on its power supply leads which are connected to the test circuit.

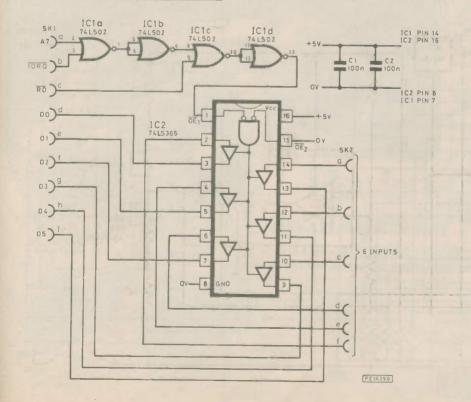
> G. Strange, Loughborough, Leics.



D7 D6 D5 D4 D3 D2 D1 D0
1 1 X X X X X X X
128 64 32 16 8 4 2 1
1 1 0 1 0 1 1
e.g. D2 and D4 are low
128 + 64 + 32 + 0 + 8 + 0 + 2 + 1=235

May be I or 0

Table 1. Showing example of IN127 command



ZX SPECTRUM BUFFERED INPUT PORT (6 BIT)

OST designs for input ports use devices such as the 74LS245 octal transceiver, but during the current chip shortages, these devices are either impossible to obtain or very expensive. There are other possible buffering chips, such as the 74LS126, but these are more difficult to design a circuit layout for.

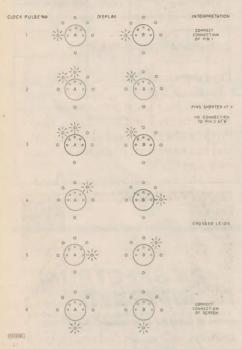
In my design I have used the 74LS365 Hex buffer/driver with gate enable inputs—the only disadvantage is that we now have only 6 inputs.

The circuit itself is very simple: the port is I/O mapped by A7 and address decoding is performed by IC1, a 74LS02. Thus when the following control lines are low—IORQ to indicate an input output operation and RD to indicate the CPU wishes to read from the I/O port indicated by the address on the address bus. The outputs of IC2 are put onto the databus of the computer. C1 and C2 are decoupling capacitors.

Since the circuit is mapped by A7 being low, an IN127 command will give 255 if all inputs are high (logic 1), as will be the case if they are left unconnected. If bit 1 (D \emptyset) is low then the result will be 254. Possible results are summarised in Table 1. Thus the result of an IN127 command in this case would be 235.

A. Moran, Reading, Berks.

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DIN LEAD TESTER

AVE you ever wondered whether all your problems might just be due to a faulty DIN lead? If so, you'll no doubt have discovered what an awkward operation it can be to test one; but here is a simple solution.

The following design will test DIN leads for open circuit, short circuit and wrong connections all in one go. Whereas with a continuity tester you need to test each pin individually, this circuit gives an immediate indication of the connections (or lack of connections) between pins at either

IC1 is a 4017, which is a decade counter with decoded outputs. It sends each pin high, in sequence, moving on to the next one every time it receives a clock pulse. For a 5 pin DIN, the sixth output is connected to reset and thus counts through 0.1.2.3.4 and 5. Six pulses are allowed to enable the screen to the tested separately (note however that this is often connected to the middle pin). The clock used to drive IC1 is produced by a standard CMOS oscillator based around IC2 (a 4011 quad NAND), the NAND inputs being shorted together as shown to act as inverters. This i.c. type was chosen merely so that fewer gates were left unused. A hex inverter would serve just as well. IC3 and IC4 are 4050 hex buffers used to drive the l.e.d.s.

The clock frequency is normally about 1kHz, providing an apparently constant display. In this mode any broken connections will immediately show up as unlit l.e.d.s. at 'B'. By pressing switch S1 the 68k resistor R1, is disconnected and the clock frequency reduced so that a more detailed representation of the condition of the DIN lead is given. Two common types of 5 pin DIN lead exist; straight through and mirror image.

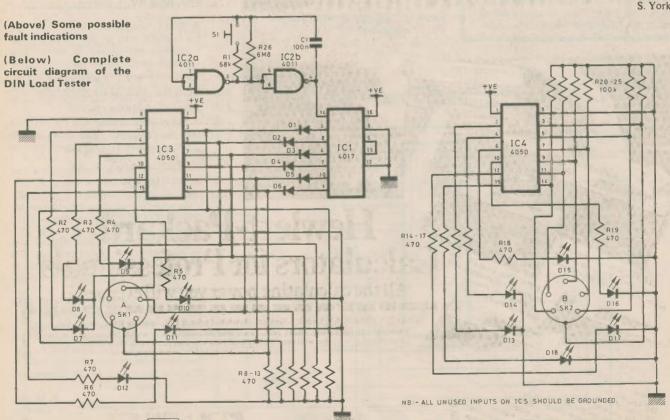
STRAIGHT THROUGH-L.E.d.s at 'A and 'B' should light in the same order.

MIRROR IMAGE-L.e.d.s at 'A' and 'B' should light in opposite orders. Crossed leads can thus be detected by incorrect orders at 'B'

Any two l.e.d.s lit simultaneously at one end in this mode indicate shorted leads at

Some sample displays are given. Using CMOS logic, the unit can be readily powered by a 9V (PP3) battery

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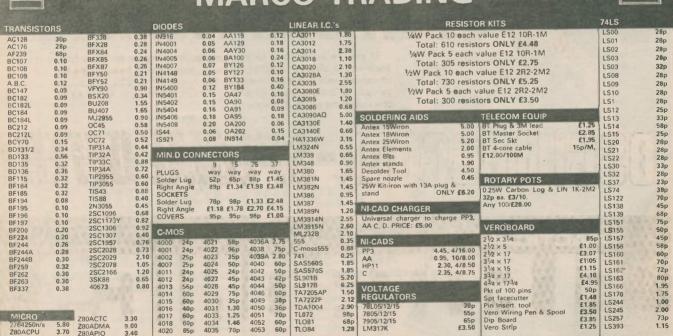
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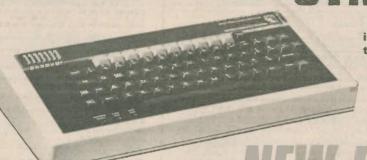
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ROBOTS neptune and mentor

THE ELECTRO-MECHANICS and the electronics of both robots have now been explained in previous parts, and the p.c.b.s and parts lists have been published. The actual construction and computer control of the robots is the last thing to be considered, beginning this month with NEPTUNE.

CONSTRUCTION

Construction starts with axis 0 and progresses upwards from there. The hydraulic cylinders of the NEPTUNE are supplied pre-assembled. First axis 0 cylinder is fitted to its sensor potentiometer, on a bracket beneath it, and then to the base plate and front plate (Fig. 6.1). There are support brackets to ensure a rigid structure and there are triangular brackets with feet on them to prevent the robot from tipping over when under load. The top slot in the rear plate is for fitting the computer interface leads to the edge connectors on the interface board. The slot beneath it is for the cables leading to the power supply which fit onto the rear plate later.

Next the top plate is fitted. Being 3mm steel this is quite heavy but this is necessary to ensure rigidity. On top of axis 0 cylinder goes the shoulder rotating axle with axis 1 mounting plate on top of it (Fig. 6.2). The weight of the arm is carried by a large thrust ball race fitted round the axle. Through the axle passes the plumbing/wiring harness which is secured to axis 1 cylinder fitted to the mounting plate.

Onto mounting rings on axis 1 cylinder the lower arms are fitted and to the upper end of these are fitted axis 2 cylinder with the upper arms attached to it (Fig. 6.3). To the end of the upper arms is fitted axis 3 cylinder which provides the wrist raising function.

PART SIX

A pair of mounting plates is used to secure axis 4 cylinder to the front end of axis 3 cylinder (Fig. 6.4). This applies to NEP-TUNE II only, where it provides wrist yaw, a function immensely useful when picking up objects lying flat or in other difficult positions. It also greatly assists spraying into corners. Yaw is a feature usually found on only the most expensive of robots used in industry. Axis 5, the wrist rotation cylinder fits to the axle of axis 4 cylinder by means of a short plate. On NEPTUNE I where there is no wrist yaw, axis 5 fits to the top of axis 3 cylinder. The gripper clamps onto the axle of axis 5 cylinder with a single set screw enabling it to be rapidly changed. The NEPTUNES are supplied with a choice of gripper types. The robot is now ready for plumbling and wiring.

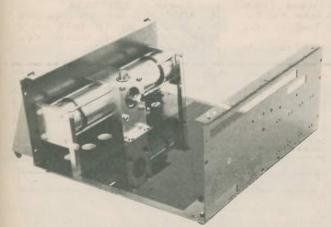
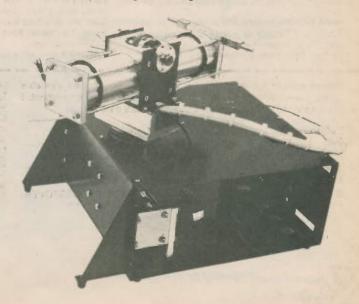


Fig. 6.1. (above): base plate and axis 0 cylinder

Fig. 6.2. (opposite): shoulder-rotating axle with axis 1 cylinder fitted to the mounting plate



ROBOTICS PROJECT

The harness is strapped onto the arms at the fixing holes with cable ties. The position for these is marked, with dabs of paint, on the harness. The pipes press into 'banjo' fittings attached to the cylinder ends with Delrin hollow bolts and the cables are trimmed and soldered to the sensor potentiometers (Fig. 6.5).

The solenoid operated valves, which control the water flow, fit with hollow bolts to a Delrin manifold (Fig. 6.6) which acts like a printed circuit board routing the water to the correct valve. The other end of the valves fit to bored Delrin bars to which the restrictors and flow rate control valves also fit (Fig. 6.7). Brackets to which the solenoid driver boards will fit are screwed to the solenoids and ensure correct alignment for the boards which clip onto the connector tags of the solenoids (Fig. 6.8). This arrangement avoids soldering to the solenoids and greatly simplifies maintenance in that the boards can be rapidly unplugged from the system. Connections to the plumbing harness

again are made with "banjo" push-on fittings and hollow bolts.

After wiring up the power supply (Fig. 6.9) and connecting to the computer interface board (no need to connect to a computer yet) the system is ready for commissioning. The sump of the hydraulic power pack is filled with water and the pump is operated with its outlet and inlet connected together with one of the plug-in pipes. This expels the air from the pipe which, after switching off the pump, is plugged into the manifold as the pressure source; the return pipe is taken from the outlet of the manifold to the sump. After pressurising the system and checking that there are no leaks the axes are tested one at a time by plugging in a solenoid driver board and the axis operated by means of a potentiometer on CN401 extend-contract connector. This will drive out most of the air. The rest of it will gradually disappear by dissolving in the water when under pressure. It then comes out of solution when returned to the sump.

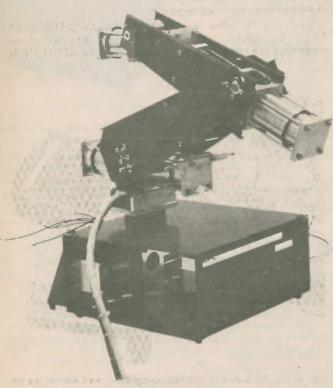
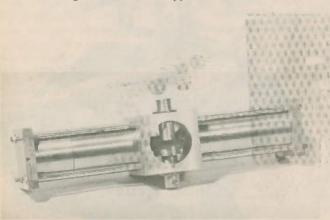


Fig. 6.3. Lower and upper arms fitted



Hydraulic cylinder assembly

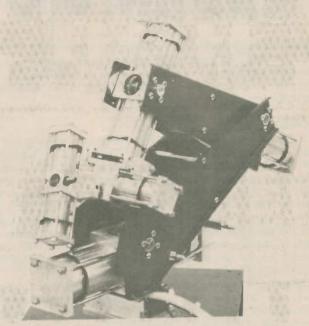


Fig. 6.4. Shoulder, upper arm and wrist assembly

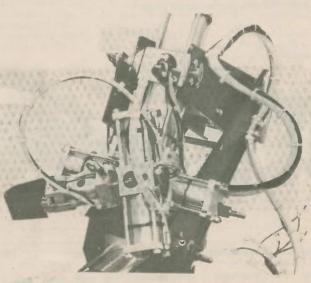


Fig. 6.5, Plumbing and wiring loom



Fig. 6.6. Hydraulic control manifold

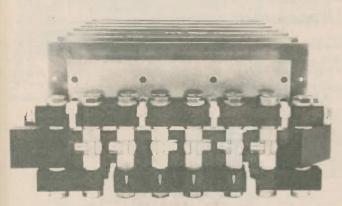


Fig. 6.7. Assembly showing restrictors and flow-rate control valves

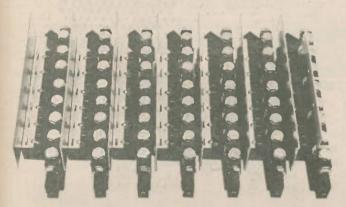


Fig. 6.8. Completed hydraulic flow-control sub-system for all seven axes

All the solenoid driver boards may now be fitted (Fig. 6.10), the computer interface board connected to the computer and the "NEPDYN" program run. This sends and returns the chosen axis between 2 points and generates, on the monitor screen, a graph of error in the axis position against time. The error is the difference between where the axis is, as measured by the ADC, and where the axis has been told to go. With the aid of this program the restrictors are set to achieve rapid convergence of the send and return graphs without any overshooting.

After setting the restrictors of each axis, the pre-sets on the solenoid driver boards are set so that sending position 0 from the computer, by means of the "NEPTROL" program, sends each axis to just before the end of its travel. The pre-sets on the interface board are set to match the positions of the simulator (Fig. 6.11) with the positions of the robot.

The interface board is next mounted over the manifold assembly (Fig. 6.12) which is then slid into the robot base and bolted down. Following fitting of side plates and covers the robot is then ready for use.

OPERATION OF THE ROBOT

Operating the robot basically consists of using POKE and PEEK instructions sent to the robot as if it were part of the memory of the computer. To move axis 0 of the NEPTUNE II

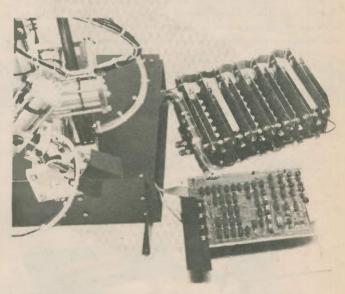


Fig. 6.10. All sub-assemblies completed and wired up for testing

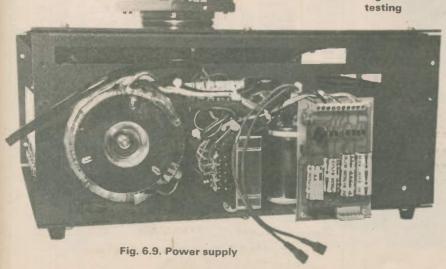




Fig. 6.11. NEPTUNE simulator arm

to position DO, the start of the 'memory' is first defined. This is also the address for the most significant byte of axis 0. The least significant byte is at the next address. On the BBC, POKE and PEEK are represented by '?' and hexadecimal numbers are indicated by '&'.

10 A=&FCOO 20 ?A=DO DIV 16 30 ?(A+1)=(DO MOD 16)*16

The data DO can be any integer from 0 to 4095 (2¹²–1) because it is a 12-bit control system. On the NEPTUNE I it is an 8-bit system so the range is 0 to 255 (2⁸–1) so only one byte is sent for each axis move. For the msb the data is divided by 16 and the remainder ignored. For the lsb this remainder is multiplied by 16 because it is the top 4 bits of the lsb that are used.

The addresses of the axes follow successively so to move axis 4 to position D4 the instructions are as below.

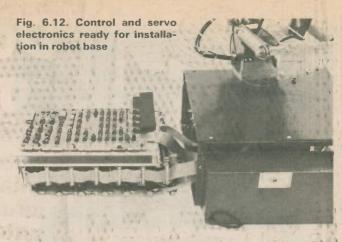
40 ?(A+8)=D4 DIV 16 50 ?(A+9)=(D4 MOD 16)*16

Similarly for axis 5

60 ?(A+10)=D5 DIV 16 70 ?(A+11)=(D5 MOD 16)*16

The servo system of the robot then makes the axis go to this position with no further computer intervention but with the ADC the position of the axis can be followed as it is moving. To operate the ADC it is written to at A+14. Data bit 7 is toggled and the multiplexer axis address set up. The axis address is in the bottom 4 data lines (see Table 1 October 1984). Axis 0 is at address 0000. The msb is read at A+17 and the lsb at A+16.

80 ?(A+14)=128 90 ?(A+14)=0 100 ?(A+14)=128 110 DAO=?(A+17)*16+?(A+16)/16



Similarly for axis 4

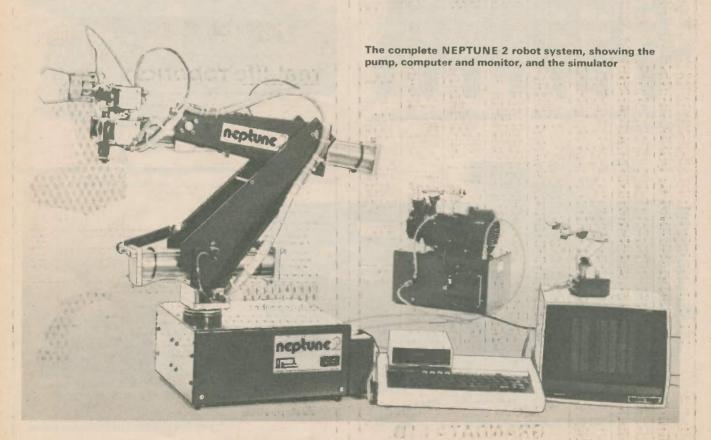
120 ?(A+14)=132 130 ?(A+14)=4 140 ?(A+14)=132 150 DA4=?(A+17)*16+?(A+16)/16

Reading the simulator is performed similarly but at the multiplexer axis address 8 bits higher so to read simulator axis 0:

160 ?(A+14)=136 170 ?(A+14)=8 180 ?(A+14)=136 190 DSO=?(A+17)*16+?(A+16)/16

If the simulator is constantly read and the data returned to the robot then the robot will follow the movement of the simulator.

NEXT MONTH: details of the assembly and use of MENTOR.







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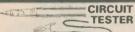
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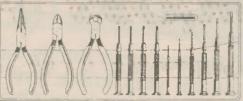
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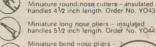


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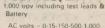
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Sequential Logic Techniques Part 5

M.TOOLEY BA and D.WHITFIELD MA MSc C Eng MIEE

AST month we carried out a detailed investigation of the operation of a universal shift, register. This month we shall turn our attention to another device which finds a wide range of applications in the digital world, the data multiplexer.

Data multiplexers, or data selectors as they are sometimes known, generally have one output and several inputs. Any one of the inputs can, by placing appropriate logic levels on its control inputs, be routed to its output, Data multiplexers thus provide us with a means of sending several different digital signals along a common signal line.

In essence the data multiplexer acts as a multi-way switch however, by virtue of its internal logic and unlike its conventional analogue counterpart, the device will only operate with digital signals.

The switch equivalent of the simplest form of data multiplexer is shown in Fig. 5.1. This two-way arrangement

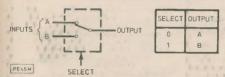


Fig. 5.1. Simplified switch equivalent of a two-way data multiplexer

is equivalent to a single-pole double throw (SPDT) logic switch. The two switch states are controlled by means of a third select input. When a logic 0 appears on the SELECT input the switch moves to position A whereas, when a logic 1 appears on the SELECT input the switch moves to position B.

The internal logic of the two-way data multiplexer is shown in Fig. 5.2.

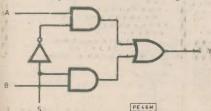


Fig. 5.2. Logic arrangement of a two-way data multiplexer

This simply consists of two two-input AND gates, a two-input OR gate and an inverter. The truth table for this arrangement is given in Table 5.1. As

Α	В	S	Υ
0	0	0	0
0	0	i 1	0
0	1	0	0
0	1	1	1 1
1	0	0	1
1	0	1	0
1 1	1	0	1
1	1	1 1	1

Table 5.1. Truth table for simple twoway data multiplexer

can be seen, whenever the SELECT input is at logic 0 the output, Y, takes the state of the A input wheras, when the SELECT input is at logic 1, the output takes the state of the B input.

By grouping together the states for which the output remains unaffected by one or other of the inputs (we shall, for obvious reasons, call these the "don't care" states!), the truth table of the two-way multiplexer can be reduced to that shown in Table 5.2.

	A	В	S	Υ
ı	0	×	0	0
1	1	×	0	1
	×	0	1	0
	×	1	1	1

x = don't care

Table 5.2. Simplified version of table 5.1

This truth table shows rather more clearly than its predecessor how the SELECT input operates; the X's in the truth table being used to denote the "don't care" states.

The switch equivalent of a four-way data multiplexer is shown in Fig. 5.3.

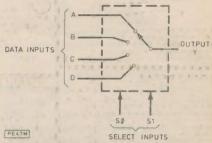


Fig. 5.3. Simplified switch equivalent of a four-way data multiplexer

Here the output, Y, can be connected to any one of the four data input lines, A to D, by means of an appropriate input on the two select lines, SO and S1. The truth table for the four-way data multiplexer is shown in Table 5.3. The corresponding Boolean expressions are:

Output	Select Inputs
Y = A	S0. S1
Y = B	SO.S1
Y = C	S0. S1
Y = D	S0.S1

We shall now investigate the operation of a practical four-way data multiplexer, the 74LS153.

	DATA	NPUTS	SELECT	INPUTS	OUTPUT	
A 0 1 1 × × × × × × × ×	B	C × × × × 0 1 ×	D × × × × × × × 1	\$Ø 0 0 0 1	\$1 0 0 1 1 0 1	Y 0 1 0 1 0 1 0 1 0 1 1 0 1 1 0 1 1 0 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1 1

x = don't care

Table 5.3. Truth table for a four-way data multiplexer

SEQUENTIAL LOGIC

THE 74LS153

The 74LS153 contains two fourway data multiplexers which have common select inputs. The pin connections of the 74LS153 are shown in Fig. 5.4. The two halves of the device

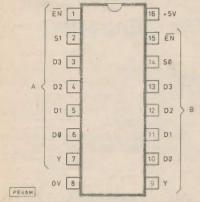


Fig. 5.4. Pin connections for the 74LS153

(referred to as A and B) are conveniently brought out to pins on opposite sides of the package; the A-side using pins 1 to 7 whilst the B-side uses pins 9 to 15. Supply connections, using the conventional pins 8 (OV) and 16 (+5V), are common to both halves of the device.

Each half of the 74LS153 has its own active low enable, EN, input. When these inputs are taken to logic 1 the corresponding outputs immediately go to logic 0 irrespective of the state of

any of the data (D0 to D3) or select (S0 and S1) inputs.

The internal logic of the 74LS153 is shown in Fig. 5.5. This clearly shows how the EN inputs are gated with the select, inverted select, and data inputs at each of the four four-input AND gates on both sides of the device. The outputs of each set of AND gates are then combined in a four-input OR gate. The 74LS153 is effectively nothing more complex than a two-pole four-way switch!

The complete truth table for the 74LS153 is shown in Table 5.4. This truth table is, of course, identical for each half of the device. When both select inputs (S0 and S1) are at logic 0, the output (Y) reflects the state of the D0 input. With S0 at logic 1 and S1 at logic 0, the output takes the state of the D1 input, and so on.

The circuit used for our practical investigation of the 74LS153 data multiplexer is shown in Fig. 5.6. It should

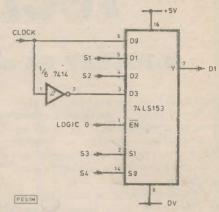


Fig. 5.6. Practical arrangement used to demonstrate the action of the 74LS153

SELECT	INPUTS		DATA	INPUTS		ENABLE	OUTPUT
SØ	S1	Dø	D1	D2	D3	EN	Υ
×	×	×	×	×	×	1	0
0	0	0	X	×	×	0	0
0	0	1	×	×	X	0	1
1	0 -	×	0	×	×	0	0
1	0	×	1	×	×	0	1
0	7 1	X	×	0	×	0	0
0	1	×	×	1	×	0	1
1	1	X	×	×	0	0	0
1	1	×	×	×	1	0	1

x = don't care

Table 5.4. Truth table for the 74LS153 data multiplexer

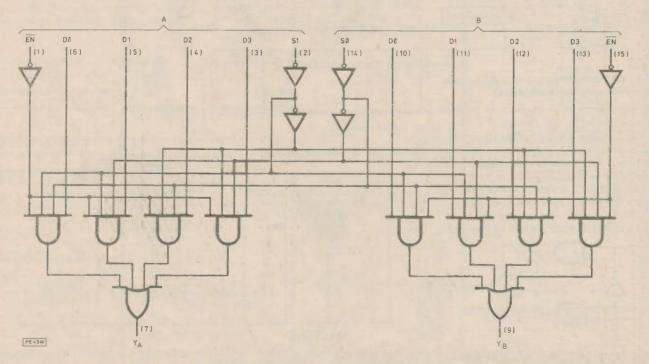


Fig. 5.5. Internal logic of the 74LS153

SEQUENTIAL LOGIC

be noted that only one half of the device is used. In order to provide four different data inputs which may be readily distinguished from one another, DO is fed from the clock whilst D1 and D2 are fed from the Logic Tutor's momentary push buttons, S1 and S2 respectively. The remaining data input, D3, is fed from an inverted clock signal derived from a 7414 inverter. The relevant half of the device is enabled by hard wiring the EN input to logic O whilst the two latching Logic Tutor switches, S3 and S4, are used to determine the state of the select inputs, S1 and SO respectively.

The 7414 should be inserted into socket D whilst the 74LS153 should be inserted into socket E with the usual orientation convention (pin-1 of each device to the respective connection marked on the Logic Tutor PCB) being observed. The following links are required:-

D1	to clock	
D2	to E3	(data input D3)
D7	to OV	(common)
D16	to +5V	(supply)
E1	to logic 0	(active low enable)
E2	to S3	(select input S1)
E4	to S2	(data input D2)
E5	to S1	(data input D1)
E6	to clock	(data input DO)
E7	to D1	(D1 indicates the
		output)
E8	to 0V	(common)
E14	to S4	(select input S0)
E16	to +5V	(supply)

(A total of 13 links)

The select inputs should initially both be set to logic 0 by appropriate adjustment of S3 and S4. The output indicator, I.e.d. D1, should then be seen to flash 'on' and 'off' in sympathy with the clock which is connected to the D0 input line.

S4 should now be adjusted to produce a logic 1 on the S0 line whilst S3 remains at logic 0. In this condition the I.e.d. will stop flashing and become extinguished. Now depress S1 to produce a logic 1 on the D1 input. The I.e.d. will become illuminated whilst S1 is held down and will become extinguished again when S1 is released.

S3 and S4 should now be adjusted to produce logic 1 and logic 0 on the S1 and S0 select inputs respectively. S2 should now be depressed to produce a logic 1 on the D2 input. The l.e.d. input will become illuminated for as long as S2 is held down.

Finally, S4 should be adjusted to produce a logic 1 input whilst S3 remains at logic 1. In this condition D1 should be seen to flash 'on' and 'off' in sympathy with the inverted clock. (i.e. when the clock l.e.d. is 'on', the output l.e.d. is 'off', and vice versa). We can summarise these observations as shown in Table 5.5.

SELECT	INPUTS	OUTPUT
S1	SO	(54)
(S4)	(S3)	(D1)
0	0	DO (CLOCK)
0	1	D1 (S1)
1	0	D2 (S2)
1	1	D3 (CLOCK)

Table 5.5. Outputs provided by the circuit of Fig. 5.7. (Note: brackets indicate Logic Tutor functions)

A PRACTICAL APPLICATION OF THE 74LS153

We shall now turn our attention to a simple practical application of the 74LS153 four-way data multiplexer. Let's assume that we wish to provide digital selection of the output frequencies of a four-stage binary counter. The four Q outputs of the binary counter can be fed to the four data inputs of the multiplexer whilst the two select inputs are fed with a two-bit control signal.

The circuit of a suitable arrangement is shown in Fig. 5.7. IC1a forms a simple relaxation oscillator in which the output frequency is determined by the time constant, CxR. IC1b forms an inverting buffer, the output of which is a rectangular pulse wave having a duty cycle of approximately 1:2 and a frequency of approximately 32Hz. This signal is then fed to the CLOCK input of IC2, a 7493 four stage binary counter.

In order to enable the normal counting sequence, the two master reset inputs, MR1 and MR2, are taken to logic 0 and the four Q outputs then have frequencies of 16Hz, 8Hz, 4Hz and 2Hz approximately.

The 7414 and 74LS153 devices should be left in sockets D and E whilst the 7493 should be inserted in socket B checking, as usual, that pin-1 aligns with B1. The following links should then be made:
R1 to R14

	(0 0 1 1	
B2	to B3	
В3	to logic 0	
B5	to +5V	(supply)
B10	to E4	
B11	to E5	
B12	to OV	(common)
B13	to E3	
B14	to E6	
B16	to D4	
D1	to logic 0	(via a 47µF 25V cap)
D1	to D2	(via a 470 ohm 0.25V
D2	to D3	
D7	to OV	(common)
D16	to +5V	(supply)
E1	to logic 0	
E2	to S3	
E7	to D1	(D1 shows o/p freq.)
E8	to OV	
E14	to S4	
E16	to +5V	(supply)

(A total of 20 links and 2 components)

The two select inputs should first be set to logic 0 using S3 and S4. The output indicator (I.e.d. D1) should then be seen to flash rapidly 'on' and 'off' with a frequency of approximately 16Hz. The three other possible settings of S3 and S4 should then be tested.

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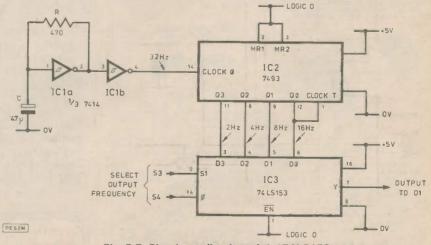
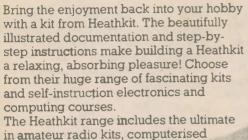


Fig. 5.7. Simple application of the 74LS153

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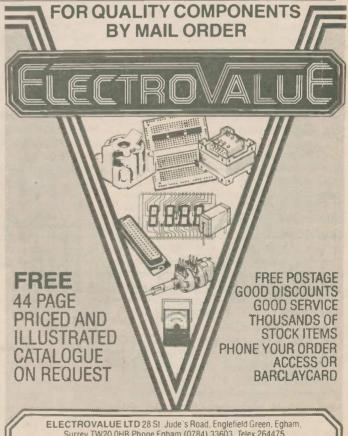
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PART TWO

THE clock signal that causes the delay chips to sample and transfer their charges from stage to stage is produced by IC9 (Fig. 6). This is a standard linear voltage controlled oscillator chip that produces a squarewave output the frequency of which is related to the value of C24, the current through VR9, and the voltage present on pin 9. The single output from IC9 needs to be split into two opposing phases as required by the delay chips. If a normal phase split were to be given then the opposing edges of the antiphase square waves would coincide. This overlap is prone to causing system noise from the delay chip outputs even though the TDA1097 is basically a low noise device, capable of a 77dB signal-to-noise ratio at a 100kHz clock frequency, though this degrades slightly with lower clock rates. The overlap on the edges of the clock is eliminated by the flip flop stage IC10 in conjunction with the NAND gates IC11a-b. C25 and R83 slow down the mutual triggering of the flip flop and gates, resulting in a twin phase output having a short delay between the respective squarewave edges. Oscillograms Fig. 7a to 7c show the 'with' and 'without' effect of the overlap elimination.

Varying the voltage applied to pin 9 of IC9 varies the clock frequency. For the automatic modulation of the clock a constantly varying voltage is produced by the low speed triangle wave oscillator around IC8a-b, and having a frequency governed by the resistance of VR7 and the value of C22. (Oscillogram Fig. 8.) Decreasing either increases the output frequency. The modulation can be switched in and out by S4, and the level varied from nil to full by the depth control VR8. C23 slightly rounds off the triangle peaks at faster modulation speeds. The modulating frequency range is controllable between about 50 milliseconds and 30 seconds, the clock frequency range is between about 12kHz and 100kHz. For a single delay chip the delay time range is thus

about 64ms to 7-68ms, cascading two delays doubles the delay times. With the modulating oscillator switched out of circuit the unit can of course be used as a standard reverb or short-echo unit, though these effects will not be so pronounced as those obtainable with the September 1984 PE Echo-Reverb unit.

POWER SUPPLY

The unit has been designed to operate from two 9 volt batteries producing +9V/OV/-9V, and drawing between 13mA and 20mA, depending on the clock oscillator rate. IC2 and IC3 though do not like a total voltage drop across them in excess of 16V, which also means that controlling voltages must not exceed this either. The positive voltage delivered to IC2, 3, 9, 10 and 11 is thus reduced to a more suitable level by the drop across the resistor R62 in the delay line bias divider network. The voltage at R62 is within limits with all i.c.s in circuit, but may rise if any of the said 5 are not in their sockets when power is applied. IC9-11 will not mind, but IC2 and 3 may object. The unit may be operated from a stabilised power supply if preferred. The acceptable range is from +5V/0V/-5V to +9V/0V/-9V. If it is necessary to run from a power supply greater than +9V/OV/-9V then two voltage regulator devices should be inserted between the power supply and the unit as shown in Fig. 9. The voltage drop across the regulators must be greater than 2V, and R62 may be replaced by a link wire.

CONSTRUCTION

The component layouts for both boards are shown in Figs. 10 and 11. The short link wires on the p.c.b.s can be made from resistor cut-off leads shaped to the correct spacing with thin nosed pliers. Sockets should be used with all i.c.s. The wiring diagram for the unit is shown in Fig. 13. Bring the

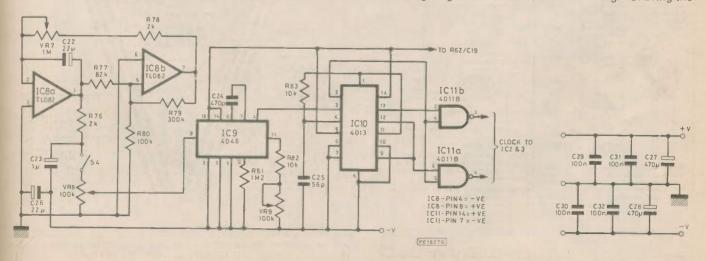


Fig. 6. Circuit diagram of the Clock Circuit

MUSIC PROJECT

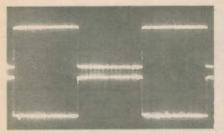


Fig. 7a. Usual appearance of two square-waves without overlap removal

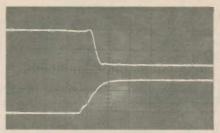


Fig. 7b. Close up of overlap

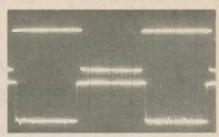


Fig. 7c. Accentuated overlap removal as used in unit

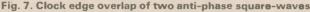




Fig. 8. Modulation oscillator waveform

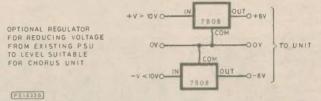


Fig. 9. Optional regulator circuit

connecting wires neatly around the edges of the p.c.b.s to the controls. The clock leads to IC2 and IC3 should be brought forward past C19, turn left at the front panel, then along to the small p.c.b., turn right and connect. Do not take them on what appears to be the shorter route across the main p.c.b. as this would direct them across some parts that might pick up any stray radiation signal. Unless you have the

eyes of an eagle, thoroughly check all the p.c.b. joins with a magnifying glass. Only after all checking has been done should the i.c.s be inserted into their sockets, remembering that IC2, 3, 7, 9, 10 and 11 are MOS devices and require the normal handling precautions. The main point being to keep yourself and equipment free of static electricity by touching a grounded source before handling them.

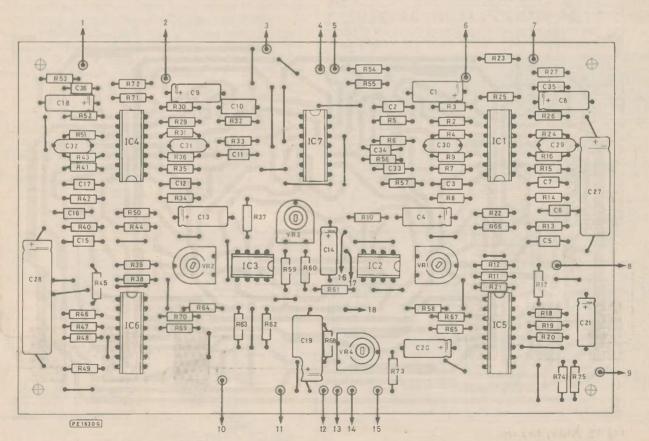


Fig. 10. Component layout of the Main Board

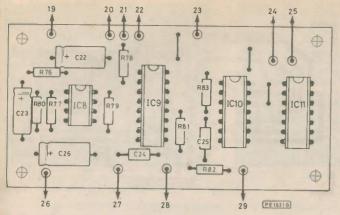


Fig. 11. Component layout for the Clock Board

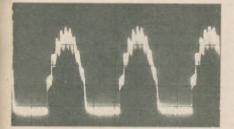


Fig. 12a. Sine-wave with VR3 unbalanced but VR1 correct

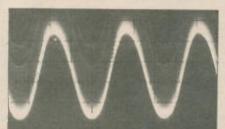
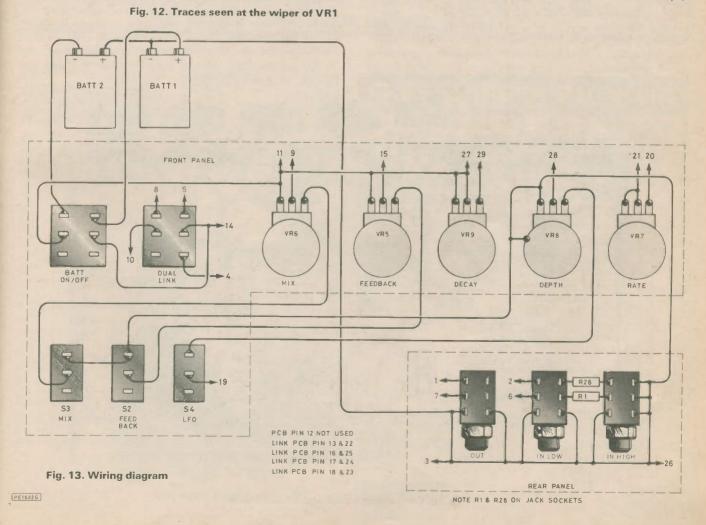


Fig. 12b. Sine-wave with both VR1 and VR3 correct

SETTING UP

This is quite straightforward and specialised equipment is not needed. First, VR1 to VR3 midway, VR4 max resistance (anticlockwise), VR5 and VR6 min, VR7 to VR9 max, S1 to S4 off. Plug in a music signal from a prerecorded source into the X1 socket. Check that the output level reaching the main amplifier used is the same as the original. Switch on S3 enabling the VCA, and bringing up VR6 a change in amplitude and tonal quality should increase. Rotating the clock oscillator speed control VR9 to its maximum resistance will slow down the delay and emphasise the double tracking effect. This will be more apparent with staccato sounds rather than mellow drawn out notes. Adjust VR3 around its midway point until minimum waveform distortion is heard, which will also coincide with the best delay effect. If an oscilloscope is available, the waveform balance will be obvious when monitoring the output at VR1 and VR2 in the presence of a strong input signal. (Oscillograms Figs. 12a and 12b.)

Switch on S4 bringing in the sweep modulator. Varying VR8 will vary the modulation depth, and VR7 will vary the modulation rate. Switch off S4, reset VR9 to slowest clock speed, VR6 to maximum level, switch on S2 for feedback enabling. Slowly bring up VR5 and a hollowness to the signal should come in. Maximise VR5 and carefully reduce the resistance of VR4 until the circuit almost goes into full feedback howl. If howl occurs, sharply



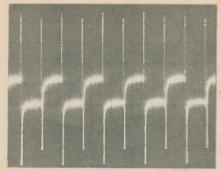


Fig. 14a. Clock residual with VR1 unbalanced (no signal)

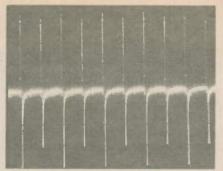


Fig. 14b. Clock residual with VR1 balanced (no signal)

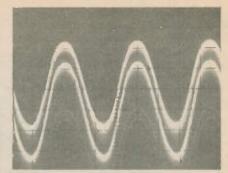


Fig. 14c. Sine-wave signal with VR1 unbalanced but VR3 correct

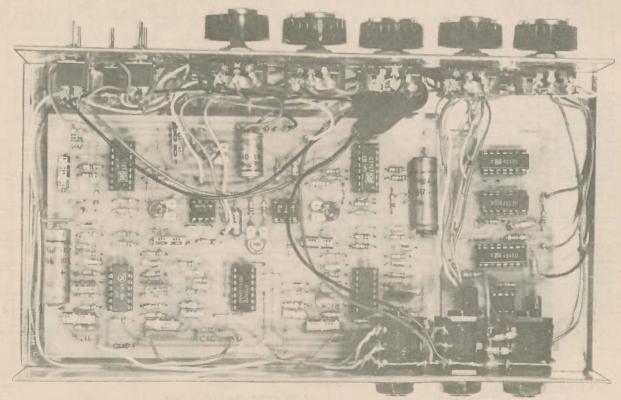
Fig. 14. Traces seen at the wiper of VR1

reduce VR4 and start again. Aim for the closest possible to the howl point. Howl is more likely to occur with strong bass notes. Switch on S1 to couple the two delay circuits in series and so produce the double emphasis. If necessary back off VR4 slightly as the increase in level may kick the circuit into howl again. If an oscilloscope is not available VR1 and VR2 should be left midway and ignored, otherwise adjust them for the best balance point of the residual clock frequency in the absence of an input signal. (Oscillograms Figs. 14a to 14c.) Switch on S4 and experiment with the various settings until familiar with the control options available, if necessary readjusting VR3 or VR4.

USE

There are no restrictions to the type of signal fed in provided that the amplitude is less than the distortion level, and that the type of music lends itself to enhancement within the factors discussed earlier and summarised below. It will soon become obvious which type of music requires which particular control setting for the best effect. This is a

matter of personal preference, but the author feels that as with any effects unit, moderation is the keyword. Certainly overemphasis of an effect is dramatic, but it is easier to become tired of an over dramatic effect than one which produces a discrete change. In general terms music having a high harmonic content, but otherwise of a simple nature, will benefit most. Mellow or full orchestral sounds will not show the same degree of change. In the first case there is insufficient harmonic information available in the signal for the effect to fully develop. In the second case, the sound is already so full that the effect will probably be lost amongst the tonal complexity unless the original sound is full of spiky waveforms. The harsher sounds of voice, drums, harmonically rich synthesiser and organ music produce excellent effects as the waveforms involved are complex. Pure sine tones and muted waveforms, especially in the lower octaves. will be less apparent. For the chorusing effect a slower clock oscillator speed is preferable as the delay time is greater, for flanging, faster clock speeds are better as the phase shift occurs then at a more marked rate and spacing.



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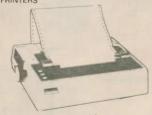


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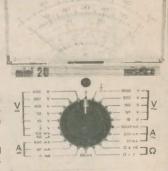
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100mA, 1A, 10A

a.c. V 10, 30V, 100V, 300V, 1000V; a.c. I 3mA, 10mA, 30mA, 100mA, 1.0A, 10Å.

a.c. I 3mA, 10mA, 30mA, 100mA, 1.0A, 10A. Ω 0–5.0k Ω , 0–50k Ω , 0–500k Ω , 50M Ω .

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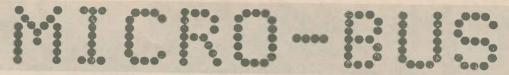
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Sir—Here is a low cost, easy to make project for use with an X/Y plotter, that can be connected to the expansion interface of the UK 101, or virtually any other micro.

The system consists of a flexible arm, equipped with two linear potentiometers and a pointer. This pointer moves over a limited surface of 20 × 20cm. The voltages, generated by the movement are a measure of the position of the pointer. Those potentials cannot be used directly for X/Y plotting, because of their nonlinear output.

A solution of that problem is found, by the application of the formula, which gives the relationship between X, Y and the angles of rotation V and H.

If now the analogue values of these angles are translated to digital, the calculation with a BASIC program becomes possible.

The BASIC program can be perceived as a limited loop with continuous conversion, so that the manual movement of the pointer can be digitally stored in memory. It permits also direct writing to a high resolution display.

Table 1 shows a typical BASIC program for illustration, and the following notes apply:

5-30 Initialisation of the PIA (A and B) for

VIA (A and B) for output.

40-180 Loop for storing data in memory 190-280 Loop for playback to X/Y

If the digitiser is used with the UK 101, it may be used with the PE-Expansion Interface published in Jan-July 1981.

I do not use the internal A/D and D/A converters, because I wanted a binary indication for the D/A output and also there is only one output in the interface. You will find the schematics joined.

The potentiometers must be of good quality and very linear. A resolution of approximately 2mm is possible on a surface of 20 × 20cm.

During storing in memory, the values of X and Y are continually displayed, and must be integer, positive and between 0 and 255

The value of L (line 100) is a multiplication constant to certify an optimum sweep between 0 and 255.

The number 255 (line 110) is added to invert the value of Y, which is negative in this area.

Line 50 in the program is the number of points you wish to fix. The movement of the pointer shall not exceed 3cm/sec

Line 255 defines the speed of playback, and

5 REM: X/Y PLOTTING ROUTINE

10 P=61340:Q=61342

15 U=61344:W=61345

17 POKEU+2,255:POKEW+2,255

20 POKEP+1,0:POKEP,0:POKEP+1,255

30 POKEQ+1,0:POKEO,0:POKEO+1.

40 INPUT "READY FOR START"; A\$

45 R=5000:S=6000

50 FOR N=1 TO 200

60 POKEP+1,60:POKEP+1,52

70 V=PEEK(P)/100

80 POKEQ+1,60:POKEQ+1,52

90 H=PEEK(O)/100

100 L=150

110 Y=L*COS(V)+L*COS(V+H):Y=INT(Y) + 255

120 X=L*SIN(V)+L*SIN(H+V):X=INT(X)

130 PRINT X,Y

140 POKER,X:POKES,Y 145 POKEU,X:POKEW,Y

150 R=R+1:S=S+1

160 NEXT N

180 PRINT"END OF LOOP"

190 INPUT"DO YOU WANT A PLAYBACK";B\$

195 IF B\$="Y" THEN 210 200 IF B\$="N" THEN 40

210 R=5000:S=6000

220 FOR N=1 TO 200

230 X=PEEK(R):Y=PEEK(S)

240 POKEU, X: POKEW, Y

250 R=R+1:S=S+1

255 FOR D=1 TO 50:NEXT

260 NEXT N

270 PRINT"END OF PLAYBACK"

280 GOTO 190

Table 1. Suggested software for calculating the angular co-ordinates

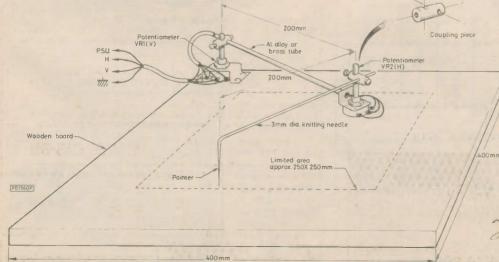
Fig. 1. Mechanical construction of the digitiser

Fig. 2. Sample of handwriting traced and stored from the

Handwerting Handwerting



Prototype digitiser



and MICROPROM

depends on the type of X/Y recorder (graphic, scope, screen).

J. Ockier. Belgium.

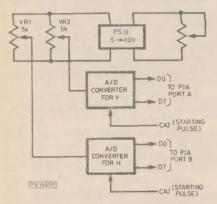


Fig. 4. Block diagram of the digitiser

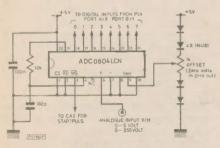


Fig. 5. The ADC channel

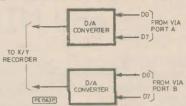


Fig. 3. Block diagram of principle

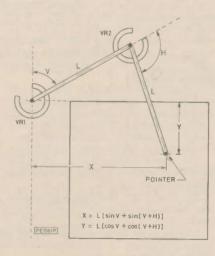


Fig. 6. A plan view showing the geometrics of the digitiser. Good quality highly linear potentiometers must be used to obtain a resolution of around 2mm

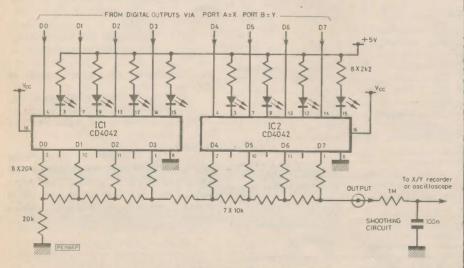


Fig. 7. Converting back to analogue for driving a plotter

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I'VE JUST had an idea. It doesn't happen all that often. So when it does I like to tell somebody about it.

I've been thinking that as we become more and more a button-pushing civilisation, our ability to communicate with each other, in the way we have been doing since the dawn of mankind, is going to take a nasty knock.

Here's an extreme instance. If and when we reach the stage where we wish our workmates good morning by punching up the salutation on a keyboard—even though we may be no more than an office apart—then sooner or later there can only be one consequence: total atrophy of the vocal chords. There's a lot in the old saying, if you don't use it you'll lose it.

And think what that could lead to in the years after you and I are laid in earth.

The end of live theatre as we know it. The death of opera. The finish of slanging matches in the House of Commons. The demise of spicy revelations at posh cocktail parties. Wholesale redundancy of bingo callers. No more air-cleaning rows between married couples. No more whispered exchanges of sweet nothings between young lovers. The start of mute TV and the passing of radio. The amputation of vocal links with people of other lands . . Try that little lot for starters. Of course, cynics will say that out of such evil there comes much good.

No more screeching prima donnas. The end of pompous party political gas. The boon of being able to get happily stoned at social functions without having to endure a load of inconsequential chitchat. No more having to bear—the twice-weekly yap of Coronation Street. No more having to study impossible foreign languages. Enhanced matrimonial bliss, made possible by the blessing of mutual silence. Goodbye, the saints be praised, to Russel Harty and Michael Parkinson; and a merciful deliverance from all that is worst in imported American TV.

* * * *

There's another aspect worth considering, now that we're diving at an ever-increasing pace into the electronic age. How is the keyboard syndrome going to affect the way we educate our children? What, for example, is to be the fate of the good old three Rs?

If you can bear a moment of near-geriatric nostalgia, let me recall Miss Richardson. She was a grey-haired lady who was totally dedicated to thumping the rudiments of good English into the skulls of her elementary school charges. She had no time for anyone unwilling to share her love of the glories of language and gems of literature. We went

through hell with the old girl. But we emerged with enriched minds.

Then there was old Bandy Andrews. I take off my hat to him as well. He firmly believed that the only worthwhile subjects in the curriculum were simple addition, division, multiplication and subtraction. These were the intellectual vitamins on which he thrived. Anyone who resisted the same diet was beyond the pale.

Finally there was Charlie Atkinson—long since departed for that great big college of calligraphy in the sky. It was he who trained us to express our callow thoughts in splendidly-rounded hands that were a joy to behold. It was his good luck to pass on before the ballpoint pen—which some people feel killed individual style stone dead—came into universal use.

"We must all accept, indeed embrace, progress as our sires did the wheel."

I agree that our education in those days was pretty elementary. But it had soul and substance. It nurtured the development of latent talents and equipped us for the years ahead. Some of us even got places on the strength of it.

* * * *

Leaving aside the emotional ramblings, let's look at things in perspective.

The computer, the microprocessor and all their derivatives, with us and yet to come, cannot fail to play an enormous part in our future lives. Nobody but an idiot would deny that. We must all accept, indeed embrace, progress as our sires did the wheel.

But I can't help feeling that we still need the basic support of established educational practices as a preliminary to hurling ourselves headlong into the fresh technologies. There is no substitute for a grounding in the three Rs. Nothing can replace the human larynx as a channel for human understanding.

Someone is bound to say that writing as I do for an electronics journal I ought to be more aware of which side my wafer is diffused. Point taken. As I said at the beginning, it's just an idea. But I still reckon that Miss Richardson, Bandy Andrews and Charlie Atkinson still have a job to do.

We're all TV critics. Whenever we moan from our armchairs we're carrying out the function, even though it's without an audience or a reward.

I'm no exception. The other night I was watching a programme called "It'll Be Alright On The Night". Presented by that brilliant jester, Denis Norden, it purports to be a collection of rejected sequences resulting from cockups by distinguished performers while recording their programmes.

It is passable entertainment and moderately funny. And, I suppose, acceptable to the gullible. But, because I have that kind of mind, I suspect that some of these boobs are specifically produced in order to provide a relatively inexpensive spin-off. Alright, such conning is perfectly legitimate if it keeps people happy and laughing.

On the other hand, if these lapses from professional standards, which betray a rather irresponsible approach to the job, are genuine, then ought we not to be just a little concerned?

Television is a voracious consumer of time, talent and, above all, money. Money, by the way, which you and I help to provide by passing our crisp oncers across the Post Office counter every year.

Thinking along those lines, it's not easy to accept as a matter of mirth—perhaps even affectionate sympathy—the banalities which such programmes offer.

Sorry Denis. I'm sure it's not your fault.

* * * *

According to a recent newspaper report, the robots of the future are going to be a lot more cuddly. Apparently 'not tonight darling' will not be a feature of their synthesised vocabulary. Sounds promising.

A spokesman for Cardiff University claims that whispering words of love and affectionate snuggling-up will present no problems for these romantic devices.

Moreover, he promises us, they will be endowded with limitless energy. Sounds even more promising.

But will there be anything in the circuitry to handle that well-known limitation—the headache?

* * * 1

In the meantime, it is reported that America has added a new category to census statistics:—Robots.

The first robot count is underway this month and will be aimed at robots on factory assembly lines. The special census form also has a section to collect information about home robots.

A more frightening rumour is the news that special robots are being seriously considered for duties as "personal" and home security guards. These robots are, it is claimed, programmed to deliver varying degrees of bodily harm; from simple electric shocks to "dismemberment".

It appears that the only obstacle is the expected multi-million dollar lawsuits that could be lodged by injured parties.—A case for Robot against Robot?

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Published on approximately the 7th of each month by IPC Magazines Limited, Westover House, West Quay Road, Poole, Dorset BH15 IJG. Printed in England by Chapel River Press, Andover, Hants. sole Agents for Australia and New Zealand – Gordon and Gotch (Asia) Ltd.; South Africa – Central News Agency Ltd. Subscriptions INLAND £13 and OVERSEAS £14 payable to IPC Magazines Ltd., "Practical Electronics" Subscription Department, Room 2816, King's Reach Tower, Stamford Street, London SEI 9LS. PRACTICAL ELECTRONICS is sold subject to the following conditions, namely that it shall not, without the written consent of the Publishers first having been given, be lent, resold, hired out or otherwise disposed of by way of Trade at more than the recommended selling price shown on the cover, and that it shall not be lent, resold, hired out or otherwise disposed of by way of Trade or affixed to or as part of any publication or advertising, literary or pictorial matter whatsoever.



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