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| watts | Tolerance | Range | available | 1－99 | $100+$ |
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| $\frac{1}{1}$ | 10\％ | 3．3MS－10MS | E12 | 1.0 p | 0.7 p |
| t | 10\％ | 1行－3．9 | E12 | 1.0 p | 0.7 p |
| $t$ | 5\％ | 4．7 ${ }^{\text {d }}$－1M 10 | E12 | 1.0 p | 0.7 p |
| 4 | 10\％ | $1 \Omega-10 \Omega$ | E12 | 71 ${ }^{\text {p }}$ | 71 P |

Quantity price applies for any selection．Ignore fractions on total order．

DEVELOPMENT PACK
0.5 watt $5 \%$ Iskra resistors 5 off each value 4．7S 2 to IMS．

E12 pack 325 resistors $\mathbf{£ 2} \mathbf{2 0}$ ．
E24 pack 650 resistors $\mathbf{\$ 4 . 2 0}$
MULLARD POLYESTER CAPACITORS C296 SERIES
$400 \mathrm{~V}: 0.001 \mu \mathrm{~F}, 0.0015 \mu \mathrm{~F}, 0.0022 \mu \mathrm{~F}, 0.0033 \mu \mathrm{~F}, 0.0047 \mu \mathrm{~F}, 2 \frac{1}{2} \mathrm{P} .0 .0068 \mu \mathrm{~F}$ $0.01 \mu \mathrm{~F}, 0.015 \mu \mathrm{~F}, 0.022 \mu \mathrm{~F}, 0.033 \mu \mathrm{~F}, 3 \mathrm{p}, 0.047 \mu \mathrm{~F}, 0.068 \mu \mathrm{~F}, 0.1 \mu \mathrm{~F}, 4 \mathrm{p}$ ． $0.15 \mu \mathrm{~F}, 6 \mathrm{p} . \quad 0.22 \mu \mathrm{~F}, 7 \mathrm{f} \mathrm{p} . \quad 0.33 \mu \mathrm{~F}, 11 \mathrm{p} . \quad 0.47 \mu \mathrm{~F}, 13 \mathrm{p}$
$160 \mathrm{~V}: 0.01 \mu \mathrm{~F}, 0.015 \mu \mathrm{~F}, 0.022 \mu \mathrm{~F}, 0.033 \mu \mathrm{~F}, 0.047 \mu \mathrm{~F}, 0.068 \mu \mathrm{~F}, 3 \mathrm{p}$ ． $0.1 \mu \mathrm{~F}$ $0.15 \mu \mathrm{~F}, 0.22 \mu \mathrm{~F}, 4 \mathrm{p} . \quad 0.33 \mu \mathrm{~F}, 6 \mathrm{p} . \quad 0.47 \mu \mathrm{~F}, 7 \frac{1}{2} \mathrm{p} . \quad 0.68 \mu \mathrm{~F}, ~ i 1 \mathrm{p} . \quad 1.0 \mu \mathrm{~F}$, $12 \frac{1}{2}$ ．
MULLARD POLYESTER CAPACITORS C280 SERIES
250 V P．C．mounting： $0.01 \mu \mathrm{~F}, 0.015 \mu \mathrm{~F}, 0.022 \mu \mathrm{~F}, 3 \mathrm{p} .0 .033 \mu \mathrm{~F}, 0.047 \mu \mathrm{~F}$ ， $0.068 \mu \mathrm{~F}, 3 \frac{1}{2} \mathrm{p} . \quad 0.1 / \mathrm{F}, 4 \mathrm{p} . \quad 0.15 \mu \mathrm{~F}, 0 \cdot 22 \mu \mathrm{~F}, 5 \mathrm{p}$ ． $0.33 \mu \mathrm{~F}, 6 \frac{1}{2} \mathrm{p} . \quad 0.47 \mu \mathrm{~F}$ ， $8 \frac{1}{2} \mathrm{p} .0 .68 \mu \mathrm{~F}, ~ I 1 \mathrm{p} . \quad 1 \cdot \mu \mathrm{~F}, 13 \mathrm{p}$ ．
MYLAR FILM CAPACITORS
$100 \mathrm{~V}: 0.001 \mu \mathrm{~F}, 0.002 \mu \mathrm{~F}, 0.005 \mu \mathrm{~F}, 0.01 \mu \mathrm{~F}, 0.02 \mu \mathrm{~F}, 2 \frac{1}{2} \mathrm{p} .0 .04 \mu \mathrm{~F}, 0.05 \mu \mathrm{~F}$ ， $0.068 \mu \mathrm{~F}, 0.1 \mu \mathrm{~F}, 3 \frac{1}{2} \mathrm{p}$ ．

100pF to $10,000 \mathrm{pF}$ 2p each
CAPACITOR DEVELOPMENT PACK
Selection of 100 ceramic and polyester capacitors， 100 pF to $1.0 \mu \mathrm{~F}, \mathbf{2} \mathbf{2} 90$. ELECTROLYTIC CAPACITORS－One Price－5p Each
Mullard C426 series（ $\mu \mathrm{F} / \mathrm{V}$ ）：25／6．4，50／6．4，100／6－4，200／6．4，320／6．4， $16 / 10,32 / 10,64 / 10,125 / 10,200 / 10,10 / 16,20 / 16,40 / 16,80 / 16,125 / 16$ ． $6 \cdot 4 / 25,12 \cdot 5 / 25,25 / 25,50 / 25,80 / 25,4 / 40,8 / 40,16 / 40,32 / 40,50 / 40$, $2 \cdot 5 / 64,5 / 64,10 / 64,32 / 64$.
Miniature P．C．mounting（ $/ \mathrm{F} / \mathrm{V}$ ）： $10 / 12,50 / 12,100 / 12,200 / 12,5 / 25$ ， $10 / 25,25 / 25,100 / 25$ ．

## POTENTIOMETERS

Carbon track $5 k \Omega$ to $I M \Omega, \log$ or linear $\left(\log \frac{1}{4} W, \operatorname{lin} \frac{1}{2} W\right)$
Single， $12 \ddagger$ p．Dual gang（stereo），40p．
SKELETON PRESET POTENTIOMETERS
Linear： $100,250,500 \Omega$ and decades to $5 M \Omega$ ．Horizontal or vertical P．C． mounting（ 0.1 matrix）．
Sub－miniature 0.1 watt，4p each．Miniature 0.25 watt，5p each．
SEMICONDUCTORS

| ACI26 15p | BFY52 | 221 P | OC81 | 15p | 2N3055 | 72p |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| AC127 15p | BSY56 | 30p | OC82 | 15p | 2N3702 | 15p |
| AC128 15p | BSX21 | 25p | ORPI2 | 47tp | 2N3703 | 14p |
| ADI40 40p | BY124 | $7 \frac{1}{2} \mathrm{p}$ | IN4001 | $7 \frac{1}{2} p$ | 2N3704 | 171 P |
| AFII5 171p | BYZIO | 30p | IN4002 | 10p | 2N3705 | 15p |
| AFII7 171p | BYZ13 | 20p | IN4003 | $11 p$ | 2N3706 | 12 p |
| BC107 14p | OA85 | 71 P | IN4004 | 121p | 2N3707 | 181 P |
| BCl08 10p | OA91 | $71 p$ | IN4005 | 14 p | 2N3708 | 10p |
| BC109 10 p | OA202 | 7 $\frac{1}{P}$ | IN4006 | 15p | 2N3709 | $11 p$ |
| BFY50 22p | OC7I | 15p | 1N4007 | 16p | 2N3710 | 12p |
| BFY51 19p | OC72 | 15p | 2N2926 | $11 p$ | 2N3711 | 14p |
| ZENER DIODES $400 \mathrm{~mW} 5 \% 3.3 \mathrm{~V}$ to $30 \mathrm{~V}, 17 \frac{1}{\mathrm{p}}$ ． |  |  |  |  |  |  |
| VEROBOARD |  |  |  |  |  |  |
|  | 0.1 | 0.15 |  |  | 0.15 | 0.1 |
| $2 \frac{1}{2} \times 3$ | 22p | 16 p | $17 \times$ | 37 （plain） | $52 \frac{1}{2} \mathrm{p}$ |  |
| $2 \frac{1}{2} \times 5$ | 24p | 24p | $17 \times$ | $2 \frac{1}{2}$（plain） | 371 P |  |
| $3 \frac{3}{4} \times 37$ | 24p | 24p | $2 \frac{1}{2} \times$ | 5 （plain） | 171 P |  |
| $3 \frac{3}{4} \times 5$ | 27p | 27p | $2 \frac{1}{2} \times$ | 3？（plain） | 15 p |  |
| $17 \times 2 \frac{1}{2}$ | 75p | $57 \frac{1}{1} \mathrm{p}$ | Pin ins | ertion tool | 471 P | 47 ${ }^{\text {P }}$ |
| $17 \times 37$ | 100p | 75p | Spotfa | ce cutter | 371 P | $37 \pm p$ |
| $17 \times 5$（plain） | － | 75p | Pkt． 3 | pins | 15p | 15p |

ROTARY SWITCHES
2P2W，IP12W，2P6W，3P4W，4P3W，22tp．
PLUGS AND SOCKETS

| Standar | in screened | 171 ${ }^{\text {P }}$ | 2.5 mm insulated |  |
| :---: | :---: | :---: | :---: | :---: |
| Standard | in insulated | 14 p | 3.5 mm insulated | 71p |
| Stereo | in screened | 35p | 3.5 mm screened | $12 \pm p$ |
| Standard | in socket | 15p | 2.5 mm socket | 71 p |
| Stereo | tin socket | 171p | 3.5 mm socket | $7 \frac{1}{2}$ |

## BRUSHED ALUMINIUM PANELS

$12^{\prime \prime} \times 6^{\prime \prime}=25 p ; 12^{\prime \prime} \times 2 \frac{1}{2}^{\prime \prime}=10 \mathrm{p} ; 9^{\prime \prime} \times 2^{\prime \prime}=7 \mathrm{p}$ ．
C．W．O．please．Post and packing，please add $7 \frac{1}{2} p$ to orders under $\boldsymbol{\ell 2}$ ． Data sheets are available for most of the components listed，and will be sent free on request．
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AVO CT471A MULTIMETER Battery operated，fully transiatorised．
Senaltivity $100 \mathrm{mn} / \mathrm{v}$ ．Meanures $\mathrm{AC} / \mathrm{DC}$ Soltages 12 mV to $1,200 \mathrm{v}$ ．AC AC／DC Current 120 A to 1.2 Amp ．Remistance 12 ohm to 120 mo HF，VHF．UHF，Voltage with multiplier 4 v to 400 v up to $50 \mathrm{Mc} / \mathrm{m}, 40 \mathrm{mV}$ to iv up to $1,000 \mathrm{Mc} / \mathrm{s}$ ．Offered in perfect condition． 856 each．Carr． 50 p ．
CRYSTAL CALIBRATORS No． 10 Small portable erystal
controlled wavemeter． Size $7^{*} \times 71^{*} \times 4^{*}$ ．Fre－ quency range $500 \mathrm{Kc} / \mathrm{s}$ ．
$10 \mathrm{Mc} / \mathrm{g}$（up to $30 \mathrm{Mc} / \mathrm{s}$ $10 \mathrm{Mc} / \mathrm{a}$（up to $30 \mathrm{Mc} / \mathrm{s}$
on harmonics）． Cali ． on harmonics），Cali－ brated dial．Power re－ quirements 300 V．D．C．
15 mA and 12 v．D．c． 0．3A．Exeellent con－ dition．

B．C． 221 FREQUENCY METERS latest retease condition．Fully teated and checked and coniplete with calibrator charts． 207．50 each．（Garr．J0p．

AM／FM SIGNAL GENERATORS
 Oscillator Test No． $\because$ precision high quality precision inetru－ ment made for the
mintstry by Airme． Frequency cover－
age $20-80 \mathrm{Mc} / \mathrm{B}, \mathrm{AM}$ age $20-80 \mathrm{Mc} / \mathrm{s} . \mathrm{AM}$
C．W．／FM．Incor－ porates precision dial，level meter，precision 12 V l．e．or $0 / 110 / 200 / 250 \mathrm{~V}$ a．c．fize $12 \times 8 \mathrm{j} \times 9 \mathrm{in}$ ．Supplied in brand new condition complete with all connectors fully tented． 845 ．Carr．\＆1

## AVO CT． 38 ELECTRONIC

 MULTIMETERSHigh quality 97 range instrument which meaoures a．c．and d．c．Voltage．Current，
Realistance and Power Output Ranges d．c． volts $250 \mathrm{mV} \cdot 10,000 \mathrm{~V}$（ 10 meg a -110 mega input）．D．e．curreut $10 \mu A-25 A$ ．Ohms． $0.1,000$ meg $a$ n．c．volt $100 \mathrm{mV}-150 \mathrm{~V}$（with current $10 \mu \mathrm{~A}-25 \mathrm{~A}$ ．Power output 50 micro－ current $10 \mu \mathrm{~A}-25 \mathrm{~A}$ ．Power output 50 micro－ supplied in perfect condition complete with clrcuit ieal and R．F．probe．285．Carr．7jp． ADMIRALTY 628 RECEIVERS
 High quality 10 valve
receiver manufactured by receiver manufactured by
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bands $100-300 \mathrm{Kc} / \mathrm{s}: 560$ bands $150-300 \mathrm{Kc} / \mathrm{a} ; 500$
 $\mathrm{Kc} / \mathrm{a}$ ．I．F． $500 / \mathrm{KHz}$ ，In－
corporates 2 R．F．and 3 I． $\mathbf{F}$ ． corporates 2 R．F．and 3 I．F．
stages，banlpass filter， stages，bamipass filter，
uose limiter，crystal con－
trolled B．F．O．calibrator I．$F$ ，output，etc．Build－in speaker，output for phones．Operation $150 / 230 \mathrm{~V}$ a．c．Size in in good working condition． 822.50 ，Carr． $\mathrm{B} 41 \underset{\mathrm{~L}}{\mathrm{~L}} \mathrm{~F}$ ．version of above．${ }_{5} \mathrm{FKHz} \cdot 700 \mathrm{~Hz}$ ． \＄17－50．Carr． 21.50 ．

TO－2 PORTABLE OSCILLOSCOPE A general purpose low
cost economy oscillo－ ecope for everyday use． $\mathbf{Y}$ amp．Band uidth
2 cPG－1 MHZ． 2 CPG－1 MERZ．Input imp． 2 meg $\Omega$ os P．F． llluminated scale． 2 in ． tube． 115 Weight 8180 ． $220 / 240$ V a．c．Supplied brand new with hand－


## TO－3 PORTABLE OSCILLOSCOPE

 ly 0－p／CM．Band
 $\mathbf{X}$ amp．sensitivity 0．9V p－p／CM．Bandwidth 1 －jeps
-800 KHz ．Input -800 KHz ．Input imp，＇3
meg 0 20pF．Time base， meg 020 pF ．Time base，
z ranges 10 cps－ 300 KHz ．
gynchrouizetion exterual，Itluminated scale $140 \times 215 \times 330$ mm ．Weight 1 ũ1b $220 / 240 \mathrm{~V}$ ．A．C．Supplied
brand new with handbook． $837-50$ ．Carr，Dop．

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USED EXTENSIVELY BY INDUSTRY，GOVERNMENT DEPARTMENTS，EDUCATIONAL AUTHORITIES，ETC． STOCK OTHER RANGES TO ORDER

＂SEW＂CLEAR PLASTIC METERS

Type Mr．85P．Atin ： 1 tin tronts．

$50 \mu-4$ $100 \mu \mathrm{~A} \ldots$. $200 \mu \mathrm{~A}$
$500 \mu \mathrm{~A}$
$500-0-500 \mu \mathrm{i}$ $300-0-\bar{u}$
1 mAA
$1-0-1$

| 1 mA | 29．60 |
| :---: | :---: |
| 1－0－1m． | 29.60 |
| 5 mA | 42.60 |
| 10 mA | 52.60 |



Type MR

| $\mathbf{3 0 \mu A}$ | 28.10 |
| :---: | :---: |
| 50－0－50 $/ \mathrm{A}$ | 28．60 |
| $100 \mu \mathrm{~A}$ | 22．60 |
| $100 \cdot 0 \cdot 100 \mu \mathrm{~A}$ | 42．87！ |
| $\underline{0} 00 \mu \mathrm{~A}$ | 20．25 |
| 1 ma | 22.00 |
| 5 mA | 22.00 |
| 10 mA | 28．00 |
| 50 ml 4 | 28.00 |
| 100 mA | 22.00 |
| 500m． | 22.00 |
| 1．A． | 28.00 |
| DA | 22.00 |

Type MR．65P． $81 \mathrm{in} \times 8 \mathrm{im}$ Ironta

| A | 23．87 | 20 V d．c． | 22.10 |
| :---: | :---: | :---: | :---: |
| $50 \cdot 0-50 \mu \mathrm{~A}$ | 28.75 | 30V d．e． | 22－10 |
| $100 \mu \mathrm{~A}$ | 22.75 | 1509 d．c | 28．10 |
| 100－0－100 L A | 22.60 | $300{ }^{\text {d }}$ d．c | 28．10 |
| $200 \mu \mathrm{~A}$ | 28.60 | $10 \%$ a．c． | 28.10 |
| 500124 | 22．871 | 30 V a．c． | 22－10 |
| $500 \cdot 0-500 \mu \mathrm{~A}$ | 82．10 | 150 V a．c． | 28．10 |
| 1 mA | $22 \cdot 10$ | 300 V a．c． | 2－10 |
| 5 ma | $52 \cdot 10$ | 300 V a．c | 10 |
| 10 ma | 22－10 | A Meter |  |
| 50 mt | 4．10 | 1 mA | 28－37！ |
| 100 mA | 管－10 | YU meter | 28.87 |
| 500 mA | 知 10 | 50 mA a．c．＊ | 2090 |
| 1 A | 42．10 | 100 ma a．c．＊ | 82．10 |
| ${ }^{\text {a }}$ | 28－10 | $\underline{200 m A ~ a . c . * ~}$ | 22．10 |
| 10A | 镍－10 | j00mA a．c．＊ | c2． 10 |
| 15A | 20．10 | 1A a．c．＊ | 22.10 |
| 20 A | 28.10 | 5i a．c．＊ | 22－10 |
| 30A | 28.10 | 10A a．c．${ }^{\text {c }}$ | 28．10 |
| j0A | 28．87！ | 10 A a．c． 20 A a．c． | 28．10 |
| by d．c． 10 V d．c． | 28.10 | $\cdots{ }^{20} 4$ a．c． | 28.10 |
| 10V d．c． | 42.10 | 30A a．c．＊ | 82.10 |

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overall $100 \mathrm{~mm} \times$ $90 \mathrm{~mm} \times 108 \mathrm{~mm}$ ． A new range of high quality moving coil instrument ments and experi－ bench applications． $3^{7}$ mlr ror acale．The meter movement is easily accesaible to
demonstrate internal working．Available demonstrate internal

in the folfowing ranges： <br> | $50 \mu \mathrm{~A}$ | 24.50 | 20 V d．c． | 88.97 |
| :---: | :---: | :---: | :---: |
| $100 \mu \mathrm{~A}$ | 84.25 | 50 V d．c． | 88.07 |
| 1 ma | 23.97 | 300 V d．c．．． | 88.07 |
| 50－0．50 $\mu \mathrm{A}$ | 44.25 | Dual range |  |
| 1－0．1mA | 88.97 | 500ma／5Ad． | 84．25 |
| 1A d．e． | 28.97 | 5V／50V de． | 24.25 |
| 5A d．c． | 48.87 | $1 \mathrm{~mA} / 10 \mathrm{~mA}$／ |  |
| 10V d．e． | 28.97 | 100 mA | 24.62 |

 signalgenerator． 5 range inexpenalve instrumen for the handyman．Oper ates on $9 v$ battery，Wide easy to read scale
800 kHz modulation $53 \times 51 \times 31 \%$ ．Complete with intructions and
leads． $87-97$ as，$P$ ．$P$ 20 p ．

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 FREAUENCY OSCILLATORS 50 Frequeney $0.20 \mathrm{Kc} / \mathrm{s}$ on 2 ranges．Outpu Supplied in perfect order． $812 \cdot 50$ ．Carr．vop MARCONI TF88G VIDEO OSCLLLATORS $0-\mathbf{j M H z}$ ．Bine gquare Wave． $\mathbf{8 4 5 \text { ．Carr．} 8 1 \text { ．}}$ LAFAYETTE TE46 RESISTANCECAPACITY ANALYSER


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A cryatal controlled hetero－ dyne frequency meter
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Me／s． Ideal for amateur uee Avallable in good used con－
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TRANSISTORS

## ${ }^{7 \mathrm{P}} \mathrm{A} \mathrm{ACl}_{\mathrm{AC}} 87$



$$
\begin{aligned}
& 30 \mathrm{P} \text { BY } 109 \\
& 30 \mathrm{BY} 24 \\
& 80 \mathrm{BY} \mid 26
\end{aligned}
$$ 100 ACY18 10 ACY 19 12 D

16 ACY 20
ACY21 20p／ACY22 20 PACY 22
$70 \mid A C Y 28$ 20 ACY 28
20 ACY 40
20p AD140 29p AD140 20p AD161
 209 BY127
28： －VALVES

## 40250 40361 40362

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40362
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$\mathrm{AC1} 26$
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ACl 54

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 1．For $8 \mathrm{SP}_{2} \overline{5}, \mathrm{SL} 6 \overline{5}, \mathrm{SL}_{5} \overline{5}, 3000,202 \overline{\mathrm{~T}} / \mathrm{C}, 202 \overline{5}$ ，
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HOSIDEN DH－08S DE LUXE STEREO HEADPHONES Features unique mech－ anical 2－way unith and fitted adjustable level
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27.971. P．\＆P． 121 p．


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First grade quality American tapes．Brand new Discount on quantities．
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5 In． $1,800 \mathrm{ft}$ ．D．P．mylar 5 Im ． $1,800 \mathrm{ft}$ ．D．P．mylar 5in．2，400it．L．P mylar 7 in ． 1,2001 t．std．acetate． inin．1，800it．LPP．acetate in． 2,400 t．D．P．mylar
$7 \mathrm{in} .3,600 \mathrm{ft}$ ．T．mylar 7 in ． $2,400 \mathrm{ft}$ ．D．P．mylar
$7 \mathrm{in} .3,600 \mathrm{ft}$ ．T．P．mylar

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Project 60．Package oftern． $2 \times$ Z30 amplifier，
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 $0.9 \mu \mathrm{sec}$ to $100 \mathrm{msec} / \mathrm{cm}$. supplied complete with all
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RESISTAMCE
ATTERDATOR
 $0-111 d B$. Connections. $\mathrm{T}_{\mathrm{an}}^{\mathrm{Un}}$ 60 anced $T$ and Bridge $T$. Impedance $+10+20+30+40 \mathrm{~dB} . \quad \begin{aligned} & \text { Frequency } \\ & +\end{aligned}$ d.c. to 200 kHz (-3dB). Frequency: 0.05 dB . +indication $\mathrm{dB} \times 0.01$. Maxi mum input less than $4 W$ (50V). Built in $600 \Omega$ load resistance with internal/external switch. Brand new $287 \cdot 50$. P. \& P. 25p. BELCO AF-5A
SOLID STATE SINE SQUARE WAVE C.R. OSCILLATOR
 $18-200,000 \mathrm{~Hz}$; Square $18-50,000 \mathrm{~Hz}$.
Output max Output max
$+10 d B$ ( $10 \mathrm{k} \Omega$ ). Operation internal
Attractive two-tove case $71 \mathrm{in} y$ sin 2 in
Price $\$ 17.50$. Carr. $17!\mathrm{p}$.
BELCO DA-20 SOLID STATE DECADE AUDIO OSCILLATOR


HIGH SENSITIVITY
A.C. VOLTMETER A.C. VOLTMETER
10 meg. input 10 ranges
 R.M.S.
Decibela $-40 / \mathrm{c} \cdot-1 \cdot 2 \mathrm{Mc} / \mathrm{s}$
to +50 dB Supplied brand new complete with leads and 230 V a.c. 817.50 Operation


## TE-65 VALVE VOLTMETER



High quality instrument ${ }_{1-5-1,500 \mathrm{~V}}$ wes. D.c. volte $1.5-1,500 \mathrm{~V}$. A.c. Volts
$1.5-1,500 \mathrm{~V}$. R . 1,000 megohms,
up up to 1,000 megohms,
e20/240 a.c. operation. Complete with probe and Inatructions. 817.50 , P. \& P. 30p. Aduitlonal
Probeg available: R.F e2.121, H.V. E2.60. R.F 230 VOLT A.C. 50 CYCLES RELAYS Brand New. 3 bets of changeover contacts at 5 amp rating. 50 p each. P. \& P, 10p ( 100 lots £40).
Quantities avalable. Quantities available.

## MULTTMETERS for EVERY purposed



7:
TECH PT-84, 1,000 O.P.V. $0 / 10 / 50 / 280 /$
$500 / 1,000 \mathrm{~V}$ a.c. and 1.c. $0 / 100 \mathrm{~K} .21 .97!$. P. \& P. $12 \downarrow \mathrm{p}$.

MODEL TR-200. 20,000
O.P.V. Mirror ncale, over-
lod protection. $0 / 5 / 25 /$
$125 / 1,000 \mathrm{~V}$ d.c.
$0 / 10 / 50 /$
$250 / 1,000 \mathrm{~V}$
a.c.
$0 / 50 \mu \mathrm{~A}$ $\begin{array}{lll}1250 / 1,000 \mathrm{~V} & \text { d.c. } 0 / 10 / 50 / \\ 2501,000 \mathrm{~V} & \text { a.c. } & 0 / 50 \mu \mathrm{~A}\end{array}$ 250 MA . $0 / 60 \mathrm{~K} / 6 \mathrm{meg}$ $\begin{array}{lll}\text { MODEL } & 500 . & 30,000\end{array}$ protection with overlos protection, mirror scale $250 / 500 / 1.000 \mathrm{~V} / 251100$ $10 / 25 / 100 / 250 / 500$ 1,000 V. a.c. $0 / 50 \mu \mathrm{~A} / 5 / 50 /$ 500 mA 12 amp. d.c.



MODEL TE-70, 30,000 O.P.V. $0 / 3 / 15 / 60 / 3001$ $600 / 1,200 \mathrm{~V}$ d.e. 0/6/30/ $120 / 600 / 1,200 \mathrm{~V}$ a.c. $0 /$ $30 \mu \mathrm{~A} / 3 / 30 / 300 \mathrm{~mA}$.
$16 \mathrm{~K} / 160 \mathrm{~K} / \mathrm{I} \cdot 6 \mathrm{M} / 16 \mathrm{meg}$
25\% P. P. \& P. 15


TMK MODEL TW-50K, 40 ranges, mirror scale. $50 \mathrm{~K} /$ Volt d.c. $5 \mathrm{~K} /$ Volt a.c. D.c.
volts: $0.125,0.25 ; 1 \cdot 25,2 \cdot 5$, 5, 10, 25, 50, $125,1250,500$. $5,10,25,50,125,250,500,1,000 \mathrm{~V}$. D.e. current: $25,50 / 1 \mathrm{~A}, ~ 2.5,5,25,50,250$



TE-900 $20,000 \mathrm{n} / \mathrm{TOLT}$ GLANT MULTLMETER Mirror scale and overload protection. 6 in full view meter, 2 colour salc. 0 ,
$2.5 / 10 / 250 / 1,000$ $5,000 \mathrm{~V}$ a.c. $0 / 25 / 12 \cdot 5 / 10 / 50 / 250 / 1,000 /$ d.c. $02 \mathrm{~K} / 200 \mathrm{~K} / 20 \mathrm{~m} / 110 / 100 / 500 \mathrm{~mA} / 10 \mathrm{~A}$ P. \& P. 2öp.


MODEL 5025. 57 ranges, giant 5 tin
meter,
polarity everse switch, Sen-
sitivity: $50 \mathrm{~K} /$ Volt D.c. Volts: $0.125,0.25,125,5,10,25,50$, $10,25,50,105,250,500,1,000 \mathrm{~V}, \mathrm{~S}_{1}$ current: $25,50 \mu \mathrm{~A}, 2.5,5,25,50,250$, $500 \mathrm{~mA}, 5,10 \mathrm{~A}$. Resiatance: $25 \mathrm{~K}, 10 \mathrm{~K}$, $100 \mathrm{~K}, 1$ meg, 10 meg. Decibels: - 20 to $+8 \overline{\mathrm{j}} \mathrm{dB}$. 212-50. P, \& P, $17_{2}^{\frac{1}{2} \mathrm{p} \text {. }}$


MODEL TE12. 20,000 $\begin{array}{lr}\text { O.P.V: } & 0 / 0 \cdot 6 ; 30 / 120 / 600 / \\ 1,200 & 3,000\end{array}$ $1 / 6 / 30 / 120 / 600 / 1,200 \mathrm{~V}$ $0 / 60 \mu \mathrm{~A} / 6 / 60 / 600 \mathrm{MA}$ $0 / 6 \mathrm{~K} / 600 \mathrm{~K} / 6 \mathrm{meg} .60$


## FTC-401

TRANSISTOR TESTER
Full capabilitie measuring $A, B$ and $1 C 0$. npn or pap. Equally adaptable for ehecking diodes. Supplied complete with instructions, battery 15p.

HONOR TE.10A, 20kR/ Yolt $\quad 5 / 25 / 50 / 250 / 500 /$
$2,500 \mathrm{~V}$
d.c. $10 / 50 / 100 / 500 /$ $1,000 \mathrm{~V}$ a.c. $0 / 50 \mu \mathrm{~A} / 2.5 \mathrm{~mA}$
 $10-0,100$ mfd. $0 \cdot 100 \cdot 0 \cdot 1$ P. \& P 15.
 $30 \mu \mathrm{~A}, 6 \mathrm{~mA}, 60 \mathrm{~mA}$ $300 \mathrm{~mA} / 600 \mathrm{~dB} \quad 15.0780 \mathrm{~K} / 800 \mathrm{~K} / 8 \mathrm{meg}$ -20 to $+63 \mathrm{~dB}, \quad 25.97$. P. \& P. 1 jp . $\begin{array}{lll}\text { MODEL TE } & \text { 80. } & 20,000\end{array}$ $0 . P .7$.
$\begin{array}{ll}1,000 V^{2} & 50 / 100 / 500 \\ 1 & 0\end{array}$ 250 , 500 a.c. $1,000 \mathrm{~F}$ d.e. $0 / 6 \mathrm{~K} / 60 / \mathrm{K} / 600 \mathrm{~K} / 6 \mathrm{M} / 5 \mathrm{ma}$. 487!. P. \& P. 13p.
MODEL TE-90, 50,000 O.P. Mirror acale, over$300 / 600 / 1,200 \mathrm{~V}$. $003 / 13 / 60 /$ $300 / 600 / 1,200 \mathrm{~V}$ II.c. $0 / 6 /$ $30 / 120 / 300 / 1.200 \mathrm{y}$
$16 \mathrm{~K} / 160 \mathrm{~K} / 1 \cdot 6 / 16 \mathrm{me}$
THK MODEL TW-20CB. Features Resettable Overload Button. Renaitivity: Folt a.c. D.c. volta: $0 \mathrm{~K} \Omega /$ $2.5,10,50,250, \quad 1,000 \mathrm{v}$

$$
\text { A.c. volte: } 0-2.5,10,50,250
$$ currents: $0-0.05,0.5,5,50,50,50,1,000 \mathrm{~V}$. D.c. Resistance: $0-5 \mathrm{~K}, 50 \mathrm{~K}, 0-500 \mathrm{~K}$, 5 meg Decibels: -20 to +52 dB . $211 \cdot 50$. P. \&

KODEL A8-100D. $100 \mathrm{~K} \Omega /$ Yolt. 5 in, mirror scale.
Built-in meter protection 0 $3 / 12 / 60 / 120 / 300 / 600 / 1,200 \mathrm{~V}$ d.c. $0 / 6 / 30 / 120 / 300 / 600 \mathrm{~V}$ a.c. $0 / 10 \mu \mathrm{~A} / 6 / 60 / 300 \mathrm{~mA} /$

 | $12 \mathrm{~dB} . \quad 212.50 \mathrm{~K} / 2 \mathrm{P} / 200 \mathrm{M}$. |
| :--- |
| +17 Cl | TMK LAB TERSTER. 100,000 6 in seale buzzer short circuit check. Sensitivity: $\mathbf{1 0 0 , 0 0 0}$ OPV d.c. $5 /$ Volt a.

 D.c. volts: $0.5,2.5,10,50,250,1,000 \mathrm{~V}$ A.c. volta: $3,10,50,200,500,1,000 \mathrm{~V}$
D.c. current: $10,100 \mu \mathrm{~A}, 10,100,500 \mathrm{~m}$ $2.5,10 \mathrm{~A}$. Resiatance: $1 \mathrm{~K}, 10 \mathrm{~K}, 100 \mathrm{~K}$ $2.5, ~ 10 A . ~ R e s i a t a n c e: ~$
10
10
meg, $100 \mathrm{~K}, 100 \mathrm{~K}$
meg. Declbels: -10 to +49dB. Plastic case with carrying handle, size 7 din $\times 6$ in $\times 3$ din. 21890 . P. \& P size 7
3 p.

SKYWOOD SW-500

$50 \mathrm{~K} \Omega / \mathrm{Volt}$. Mirror scale BC Volt
$0.6 / 3 / 12 / 30 / 300 / 600$ AC Volts $3 / 30 / 300 /$ 600 . DC Current 20uA/6/60/600mA. Reslstance $10 \mathrm{~K} / 100$ K/1Meg/10 Meg. De.
27.50. P. \& P. I р.
$270^{\circ}$ WIDE ANGLE 1 mA METERS MW1-6 $\quad$ G0mm
e8.87t.
square
square square 44-97, P. \& P square
extra.


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4 Bands covering $550 \mathrm{KHz}-30 \mathrm{MHz}$. B.F.O with instructions. $115-75$, Cs.cr. B7! 37 p.

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Large quantity available for EXPORT Excellent condition. Enquiries invited.


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COMM OHICATION RECEIVER
4 Bands covering $55 \mathrm{KHz}-30 \mathrm{MHz}$. FET, s Meter, Varlable BFO for SAB. Huilt in Speaker, Bandspread, Sensitivity Control.



LAFAYETTE
HA- 600 RECEIVER

Genctal coverage $150-500 \mathrm{KHz}, 500 \mathrm{KHz}$ 30 MHz . FET front end, 's mech. filtere, limiter, \& Meter, Bandspread. RF Gain. 15 in : 97 m \% 8 in. 18 lb . $220 / 240 \mathrm{~V}$ a.c. or 12. d.c. Brand new with instructions 445. Carr. 30 p

## 

$3 \cdot 5-4,7-5 \cdot 3,14-14 \cdot 35,21-21 \cdot 45,28-29.7$ filters, product delector, variable BFO filters, product detector, variable BFO,
y a.c, or 12 V d.c. 15 in 9 in $8\{\mathrm{in}$. 181 b . Brand new with instructions. e57.50. Carr. pail ( 100 KHz ('rystal $£ 1.97$ ! exira).

FULL RANGE OF TRIO EQUIPMENT
EDDYSTONE VHF RECEIVERS MODEL 770R. 19-165 Mc/s. Excellent condition. 8150

VOLTAGE STABLISER TRANSPORMERS $180-260 \mathrm{~V}$ input. Output 230 V . Availabl 50W or 225 W . 212.50 .

## AUTO TRANSFORMERS

$0 / 115 / 230 \mathrm{v}$. Step up or atep down. Finl obrouded.

$$
\begin{aligned}
& \begin{array}{lll}
1,000 \mathrm{~W} . & 27.25 . & \text { P. \& P. } 371 \mathrm{p} . \\
1,500 \mathrm{~W} . & 88.97 . & \mathrm{P} . \& \mathrm{P} .42 \$ \mathrm{p}
\end{array}
\end{aligned}
$$

SOLID STATE VARIABLE A,C VOLTAGE REGULATORS
 Compact and panel mount ing. Ideal for control of
lamps, drills. electrical lamps, drills. electrical
appliances, etc. Input $230 / 240 \mathrm{~V}$ a.c. Output con. tinuoumly variable fron 20 V to 230 V . Model MR2305 5A 88 K 46
$\times 43 \mathrm{~mm}, 88.371$. Model MR2310 IOA

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HIgh quality ceramic construction. Windings embedded in vitreous enamel, Heavy duty brush riper. Continuous rating. Wide range estock Single hole fixing, In. dia. shafts. Bulk quantities available. WATT. $10 / 25 / 50 / 100 / 250 / 500 / 1,000 / 1,500 / 2,500$ or 5,000 ohms, $72!\mathrm{p}$. P. \& F. Tlp. 50 WATT. $10 / 25 / 50 / 100 / 250 / 500 / 1,000 / 2,500$ or 5,000 ohms, $21 \cdot 05$. P. \& P. $7!p$. 100 WАTT. $1 / 5 / 10 / 25 / 50 / 100 / 250 / 500 / 1,000$ or 2,500 ohms, $21 \cdot 37$. P. \& P. $7 \leq p$.
ADVANCE TEST EQUIPMENT rand now and boxed in originalisealed cartons 100 79 , DEF HILLIVOLT METER, D.c. 10 mV to 3 V . Current 0.01 mA to 0.3 mA. Resiatance 1 ohm to 10 megohm 125.

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12 polt Car Battery Trickle Charger. Made it Japan, this is very small and neat. Regular use will keep your car batter in good trim throughout
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Mind Inimeraion Heater, 350 w 200/240r. Boill full cup in about To minuter. Ube any socket or tes, baby's lood, etc. 21.25 , post and insurance 14 p . 12 F . car model also a vaileble 21 .
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Willdimincandeacent lighting up to 600 w . from full briliance to out. Assenibled and wired ready to inetall 28.

AUTO-ELECTRIC CAR AERIAL with dashboard control swltchfully extendable to 40 in . or fully
retractable. Suitable for 12 y retractable. Suitable for 12 V complete with fitting instructions and ready wlred dashboard switch. 25.95 plus $2 \overline{5}$ p post and ins COMPUTER TAPE $2,400 \mathrm{ft}$ of the best magnetic tape money can buy. Made by L.M.I., lin. wide almost unbreakable and on a $10{ }^{\text {in }}$ in. metal computer spool. Users have claimed successful results with video ay well as sound recordings 81 plus 33 , post

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HORSTMANN "TTME E SET" SWITCH to a warm house without it costing you a fortune. You can delay the gwitch on time of your electric fires, etc., up to 14 hours from setting time or you can use the awitch to give a boost on period of up to 3 hours. Equally sultable to 8pecial snip price $21 \cdot 50$. Post and ins. 23p.

IHOUR MINUTE TIMER
Made by famous \&mithe company, these have is large clear dial, size 4 in,$\times 3$ in., which can lie set in minutes up to 1 hour. After presct periol the bell ringe. Ideal for processing, a memory jogger or, by adiding simple lever, would operate micro-awitch,


THE FULL-FI STEREO SIX


The amplifier
sensation of the year You will be anazed at the fullness of reproduction and at the added qualities your records or tuner will re. produce. Builtinto metal and teak finished to blend with Hodern furnishings, this amplifier uses an ategrated solid atate circuit with an output power of 6 watts R.M.S. split over the two channels. The amplifier is ideal for use with normal pick-ups and tuners, it has a double wound mains transformer and ganged volume and tone controls-also switching for Mono to Stereo, tuner or pick.up. Other controls include "treble lift and cut", "balance" and separate mains on/off switch. Price is 59 plus 38 p post and insurance

| 1 pole | 33 p | 33p | 33p | 33p | 38p | 33p | 33p | 33p | 33p |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| 2 poles | 33p | 33p | 33p | 33 p | 33p | 33 p | 33p | 55 p | 55p |
| 3 poles | 33p | 33p | 33p | 33 p | 55p | 55p | 550 | $75 p$ | 75p |
| 4 poler | 33p | 33p | 38p | 55p | 85p | 55 p | 55 p | $95 p$ | 95p |
| $\overline{3}$ polea | 38p | 38p | 55p | 55 p | 75p | 750 | 75 p | £1-15 | 21.15 |
| 6 poles | 33p. | 55p | 55p | 55p | 75 | 75p | 75 p | 21.35 | 21.35 |
| 7 poles | 55 p | 55p | 55p | 75 | 95p | 85p | 95p | £1.55 | 21.55 |
| 8 poles | 55p | 55p | 55p | 750 | 950 | 95p | 95p | 21.75 | 21.75 |
| 9 poles | 55 p | ${ }^{55} 5$ | 75 p | 75 p | 21.15 | 21.15 | 21.15 | 21.95 | \&1.05 |
| 10 poles | 55p | 65 p | 75 | 95p | 21.15 | 21.15 | 21.15 | ¢2.15 | e2.15 |
| 11 poles | 550 | 750 | 75 | 95p | 21.35 | 21.35 | 81.85 | 48.35 | 88.85 |
| 12 polem | 55 p | 76p | 75p | 95p | 21.85 | 21.35 | 21.85 | 42.55 | 28.55 |

## SPARTAN Portable

 LOUR RADIOLong and medium wave 7 translator, size 6 in. than win. With larger very good tone. Built-in very goom tone. Built-l scoplc aerial for distant

stations. A real bargain complete with leather casc, calry wling, earplug and case. 28.75 plus 25 p post and ins.

## MULTI-SPEED MOTOR

Replacement in many well known 500,850 , and $1,100 \mathrm{r} . \mathrm{p} . \mathrm{m}$. from either or both of the nylon sockets (where the beaters of the food mizers normally go) and $8,000,12,000$ and 15,000 r.p.1n. (ideal poliahlng speeds) from the main drive shaft. Very nowerful and useful motor size Price gop plus o3p post and ing


MAINS OPERATED CONTACTOR
$220 / 240$ V 50 cycle solenohl with laminated core so very silent in operation. Closes 4 circuits each rated at 10 A . Extremely well made by a Overall size $2!$ g 2 in. 21 each.

DOUBLE ENDED MAINS MOTOR
On feet with holes for serew. down fixing. To drive modets, oven, blower heater, etc. SOp each, plus 28 p post and insura
0.005 mFd TUNING CONDENSER

Proved design, ideal for straight or reflex eircuits 13p each, $\mathbf{k 1}$ - 20 doz.


ELECTRIC CLOCK
WITH 25 AMP SWITCH Made by Smith's, these unite are a fited to many top quallty
cookers to control the oven. The cookers to control the oven. The
clock is nains driven and trequency controlled so it is exquency controlled so it is exdials enable switch on and ofll
time to be accurately get. Ideal tIme to be accurately set. Ideal for awltching on tape recorders. Offered at ouly; fractlon of the regular price-new and unuaed only
post and insarance 14 p . post and insurance 14 p .

## FLUORESCENT CONTROL KITS


#### Abstract

Each kit comprises seven items-Chok tube ends, starter, starter holder and 2 tube clips, with wiring instruct ions. Suitable for normal fluorescent tubes or the new 'Grolux' tubes for fish tanks and indoor plants. Chokes are super-silent, mostly resin filled. Kit A- $10 \mathbf{0}-20 \mathrm{~W}, \mathrm{Et}$. Kit $\mathrm{B}-30-40 \mathrm{~W}$, \&1. Kit (1-80w, $21-20$. Kit $\mathrm{E}-30 \mathrm{JW}, \mathbf{2 1 . 2 0}$. Kit for 8 ft 1 '2 5 W tube $\mathbf{8 1 . 7 6}$. Kit MFl is for 6 in 9 in and 12 in miniature tubes, is. Kit MF: for 2Iin minature tubes, ell. Kit Postage on Kits A and $\mathbf{B} 23 \mathrm{p}$ for one or two kits then $23 p$ for each two kits ordered. Kits C, D and E 3 p on first kit then $18{ }_{p}$ for each kit ordered. Kit F 33p then 23p for each kit each tro kits ordered on first kit then 18p on each to ${ }^{\circ} \mathrm{o}$ kits ordered


## BLANKET SWITCH

 Double pole with neon let Ito aide bo luninous in dark,deal for dark room light or use with waterproof element -ur

## BLANKET SIMMEASTAT

 Although looking like, and fitted as anordinary blanket suitch, this is in orderice for switching on for tarying time perlods, thus giving a complete eontrol from of to full heat. Although suitable for controlling the teniperature of any other appliances using up to 1 A . Listed at $\mathbf{2 1 . 4 0}$ each we offer thesc while our whocks lant at only 65p each.

REED SWITCHES
Glate encased, wwitches operated by external magnet-gold welded contact We can now offer 3 types:
Laterare. lin long a approzimately in diameter. Wlll make and break up to 1 A up to 300 olte. Price 18 p each, 81.20 dozen.
break current of up to 1 A , voltages up to will volle. Price 10 p each, 90 per dozen.
Fiat. Flat type, 2in long, just over hin thick, datteued out, so that it can be fitted into a maller apace or a larger quantity may be packed nto a square solenojd. Rating 1 amp 200 volts. Price 30 p each. es per dozen. mant ceramic magnets to openate these reel HIGHCAPACITY ELECTROLYTICS Brand new, not ex-equipinent.
00 mfl ajv op cach 60 p doz.
50 myd . $50 \mathrm{~V}, 16 \mathrm{p}$ each $\mathbf{1 1} .65 \mathrm{~d}$.
400 mifd. $40 \mathrm{v}, 29 \mathrm{peach} 29.30$ doz.
$500 \mathrm{mid} .12 \mathrm{~V}, 10 \mathrm{p}$ each $\mathbf{2 1 . 0 5}$ doz.
00 mid. $25 \mathrm{Y}, 18 \mathrm{p}$ each 21.00 doz.
500 mild .50 V ; 28 p cach 22.40 doz.
$500 \mathrm{mid} .350 \mathrm{~V}, 48 \mathrm{p}$ each 3450 do
$1000 \mathrm{mfd} .12 \mathrm{~V}, 15 \mathrm{p}$ each $\$ 1.50$ doz
1000 mfd . $18 \mathrm{~V}, 17 \mathrm{p}$ each $\$ 1.70$ daz
$1000 \mathrm{mdd} .64 \mathrm{~V}, 8 \mathrm{87p}$ each $84 \cdot 70 \mathrm{dk}$
$2000 \mathrm{mdd} .25 \mathrm{~V}, 34 \mathrm{p}$ each $\mathbf{1 4} \mathbf{3}$ doz.
2000 mid. 12 V , 24 p each 48.40 doz
$10,000 \mathrm{mfd} .6 \mathrm{~V}, 29 \mathrm{peach} 48 \mathrm{doz}$. 10,00 mal 48 g each $24.50 \mathrm{~d} 0 z$
$15,000 \mathrm{mld}$. $10 \mathrm{~V}, 48 \mathrm{~g}$ each 55 doz .
$90,000 \mathrm{mfd} .8 \mathrm{~V}, 81 \cdot 10 \mathrm{cach} 210 \mathrm{doz}$
$70,000 \mathrm{mfd} .13 \mathrm{~V}$, 82 each 280 doz
priaing 129 BATRERY CHARGER KIT- compriaing $230 / 40$ maing transformer with 3 amp secondary and 3 amp rectifer $81 \cdot 15+$ 2 2 p post. double-wound $230 / 240 \mathrm{~V}$ mains transformer with full wave rectifier and $2000 \mathrm{~m} / \mathrm{f} / \mathrm{d} / \mathrm{smoothing}$ Price 81.40 .
8OFOTONE ETEREO CARTRIDGE. Turnover type, ref. No. 19 T1. This fits most British pickups and is a really excellent reproducer. Limited Ifuantity, E1.
5 AMP 3-PII
SOCKETs. These are alwayy goor miock, you never know when youl will need som ramous make, brown bakelite, standard size 12 for 65 p plus 23 p post
 cream, less switch. for il.

解 to have just taken delivery of approximately 10 tons of bakelite in varying thicknesses from 2 in to a few thou. If you have a need for any of this then we would be glad to supply. The thickest is bed for a motorised unit. Medium thickness is useful for front panels of instrunent etes Cut to your size price is 30 p per lb . plus 30 p cutting charge plus carriage. mounting, brown bakelite. Manle hy fantons Hlaker. $13 p$ each or si- 20 dozel.
100 A8sORTED SILICON RECTIFIES G.P. AND 8WITCHMG DIODES. Small aud very smal

20 AMP ELECTRICAL PROGRAMMER
Loarg in your wloep: Have Radio playing and
kettle boiling as you awake-switchon lights to
ward off intruderg-have warm house to come
home to. All these and many other thlngs you cal
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Total distortion $1 \mathrm{kHz} 9 \mathrm{~W} 0.5 \%$. Input sensitivities-CER, P.U. 100 mV into $3 \mathrm{M} \Omega$; Tuner lomv into
$100 \mathrm{~K} \Omega$. Tape 100 mv into 100 k Overload' Factor-Better than 26 dB Signal to noise ratio- 70 dB on all signal to noise ratio-70dB on all Mk. II (MAG. P.U.) Specification same as Mk. I, but with CER. following inputs: Mag. P.U. CER. P.U Tuner

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## ONE GOOD REASON

There are all sorts of reasons why people build electronic equipment for themselves. A very good one is, simply, that unless they do, they go without!

No wild exaggeration, this. While the semiconductor industry can turn out vast quantities of thought-provoking circuit devices-orginally developed for professional applications, it is true-is it not strange that equipment manufacturers have not seized upon these to embody in a host of imaginative functional products for the domestic consumer?

Oh yes, for sure the radio, television, and audio equipment business is well saturated, as the shop windows and showrooms in every high street testify. But the very proliferation of traditional entertainment products from both home and overseas factories induces a lop-sided view of electronics and what it can do for everyman and his wife. For instance, light and heat sensitive semiconductors, and power switching thyristors and triacs, are all crying out for more general use; to say nothing of logic systems based on miniature integrated circuits which offer possibilities for programming routine switching operations within the home.

There has been plenty of pie-in-the-sky talk of the electronics-run home of the future. When will the big breakthrough occur?

While prodding the commercial world to venture into these unusual and as yet scarcely explored domestic regions, we do see that this is not so simple nor (perhaps) as profitable as satisfying mass market needs for standardised conventional products like radio and audio equipment. Many installed automatic systems, such as intruder detectors, and environment sensing and controlling equipments, have to be tailored to suit specific needs and situations. And coping with a number of possible combinations from a wide range of units in order to build up an ideal installation for one customer would give the retailer some headaches, no doubt.

This is, of course, where we came in: if you do require something rather special in this particular line of electronics, the chances are you will have to build it yourself. This is just one further demonstration of the paradoxical situation we now have, and which arises directly from the highly productive semiconductor industry: the general availability of mass produced, efficient and versatile devices is helping in the preservation of individual craftsmanship.
F.E.B.

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BOOK REVIEWS

## PRICE INCREASE

As from next month, the price of Practical ElecTRONICS will be 20p (4s). We regret the necessity for this increase, which is due to rising production costs.

Our May issue will be published on Friday, April 16

[^1]Create living colour that "moves" with the mood of your music.

## P.E. AURORA is a controlled lighting system that can be as simple or as complex as you like to make it.

The selected audio frequency ranges can be "coloured" and the lighting arranged in whatever domestic decor


SOUND controlled colour light displays can be arranged to provide several kinds of visual effects some of which have been exploited for television


Fig. I. Basic eight channel thyristor switching system used to operate a 16 -lamp matrix of P.E. Aurora


## PART 1 By

## M.J.HUGHES M.A.

The P.E. Aurora system was specially commissioned by Practical Electronics and is the result of close collaboration with M. J. Hughes, M.A., who designed the electronics, and M. Leonard, A.R.J.B.A., who was responsible for the artistic presentation of this light display shown at the "Audio \& Music Fair" and the
"Electric Theatre" exhibition.

## THYRISTOR OR TRIAC CONTROL

The heart of the system to be described is a d.c. voltage controlled phase shifter, coupled to a trigger circuit, which in turn fires either triacs or thyristors early or late within the mains a.c. waveform. The controller's input is of high impedance and has at linear control over input voltages ranging from 0.5 V 101.0 V d.c.

The input is 100 per cent isolated from the output, thus the control voltages can be derived with safety from many forms of semiconductor circuitry. Two such circuits will be described in detail: a narrow band filter unit-for sound to light control, and a self programming digital unit which provides constantly changing light patterns.

Other input circuits, which will be discussed later, include tape control (using at conventional tin or cassette tape recorder) and several types of optical feedback control.

The system to be described will be based on eight individual control channels supplying a matrix of 16 lamp nodes, but individuals can tailor their systems to suit the application or their pockets. The basic system is shown in block form in Fig. 1.

## DESIGN SPECIFICATIONS

As the original intention was to make the "P.E. Aurora" a versatile piece of equipment the following design parameters were self-imposed:

1. Ultimate a.c. power control should be by readily available thyristors or triacs and the

equipment should interface with as wide a range of trigger requirements as possible, in conjunction with the a.c. mains frequency.
2. Either triacs or thyristors could be used without any change in circuitry, provided they are capable of operation from the voltage and current source of the switching circuit.
3. The power side of the controller should be isolated from the input for safety reasons-this isolation should not be by optical means (which is quite often specified) because it presents difficulties in producing a simple mechanical construction.
4. Phase angle control should be over a range of as near 180 degrees as possible to obtain full lamp brightness and as near full extinction as possible.
5. Input signal requirements should be as wide as possible and be such that the equipment can be used with semiconductor circuitry.
6. Simple unstabilised power supplies should be used. All circuitry should be simple, should use low price components, and should need no specialised test equipment for setting up, apart from a multimeter and possibly an audio signal generator.
7. Perhaps the most difficult of the specifications to achieve; that the lamp brightness should appear linearly related to the input control signal.
All the above parameters have been met in the equipment to be described.

## FREQUENCY LOCKED SWITCHING

Fig. 2 shows a block diagram of a single control channel. All thyristor or triac phase control systems should be accurately locked to the mains frequency so that linear control may be effected by firing the device early or late within a single mains frequency cycle or half-cycle.

The triacs require a trigger pulse every positive and negative half-cycle of the mains while a thyris-tor-a unidirectional switching device-requires trigger pulses during positive half-cycles only. The sync pulse generator produces a single positive going pulse at the start of every positive and negative going half-cycle of the mains frequency. This pulse is applied to all channels in parallel (the present generator will satisfactorily drive up to 10 control channels).


Fig. 3. Circuit diagram of the power supply and sync pulse generator

Considering a single channel; the arrival of this pulse fires the monostable multivibrator, the output of which rises to approximately +10 V and dwells at this level for a period which is set either by the manual control or the input d.c. control signal. It is this dwell time that controls the phase angle of the final trigger pulse and is designed to be in the range of 2 to 9 ms (this gives a range of firing angles of approximately 36 to 160 degrees).

After the dwell period the output of the monostable falls back to zero volts and this negative going transition is detected and amplified by the pulse shaper, which is coupled to the primary winding of a simple pulse transformer. This provides isolation between the mains and low voltage parts of the circuit. The secondary of this transformer is directly coupled across the cathode and gate of the thyristor or main terminal I and gate of the triac.

Trigger pulses will arrive at the transformer every 0.01 sec and thus will fire a triac on every half-cycle. If a thyristor is used only alternate pulses will fire the device pulses arriving during negative excursion half-cycles will be ignored.

## POWER SUPPLY AND SYNC PULSE GENERATOR

As the power supply and sync generator are closely coupled to the mains transformer, both units are shown in Fig. 3. T1 is a straightforward mains transformer having two separate secondary windings each providing 12 V a.c. One of the windings rated at 500 mA is connected to a standard bridge rectifier comprising diodes D1, 2, 3, and 4. The smoothed output of this supplies sufficient power to drive all the circuitry required for the eight channels.

The inductors L 1 and L 2 together with C1 provide a satisfactory degree of interference suppression. The rating of fuse FS1 will depend on the total power the controller will eventually be driving. In the case of the prototype a 5 A fuse was sufficient. Later we will deal with modifications necessary for higher power operation.

The main switch S 1 only serves to isolate the electronics from the mains-it does not disconnect the main power to the lamps owing to problems in obtaining a suitably rated panel switch of reasonable mechanical proportions.

The second winding of $T 1$ is connected to a bridge comprising four germanium diodes-D5, 6, 7 , and 8 . This provides a full wave rectified signal across the nominal load R1.

For those constructors having access to an oscilloscope. approximate waveforms are shown on the circuit diagram. Diode D9 is a small signal silicon type connected in a forward biased direction. The 600 mV forward drop across this device serves to clamp the full positive excursion of the bridge producing a waveform closely resembling a square wave with fairly fast negative going edges. This waveform is inverted and its level restored to approximately 10 V (off load) by transistor TRI.

using S.C.R.
Fig. 4. Waveform timing diagram as measured on an oscillioscope. Typical amplitudes are shown. All levels are measured relative to the zero voltage rall. Waveforms ( g ) and (h) show the extremes of fring angle, 36 to 160 degrees

The output is a 100 Hz sync pulse which is then applied to all the monostable stages for triggering the thyristors. On full load the amplitude of the positive going pulses at the collector of TR1 falls to approximately 5 V .

The waveform timing diagram shown in Fig. 4 shows the relationship of sync pulses to the original mains waveform ( $\mathrm{a}, \mathrm{b}, \mathrm{c}$, and d).
However, due to the trigger sensitivity of the monostables (which require approximately 4 volts for reliable triggering) the monostable does not fire until the sync pulse reaches this voltage which occurs almost exactly at the moment the mains waveform crosses the zero voltage line (Fig. 4e).

## MONOSTABLE AND TRIGGER CIRCUIT

Fig. 5 shows the circuit of the monostable and trigger for a single channel. In this system eight such circuits are required; for other systems more or fewer can be built.

TR3 and TR4 form the main monostable, these being cross coupled by C5 and R11. Sync pulses are applied to the base of TR3 via C4 and D10. In the absence of such pulses TR4 is normally "on", its base being returned to the positive rail by R9 and the parallel combination of VR1 (a preset potentiometer), VR2 (the manual control) and TR2.

On the arrival of a sync pulse at TR3 this transistor switches on rapidly; the negative going transition at its collector is transmitted via C5 to TR4 which turns off and stays off for the duration of the time constant of C5 together with R9. VRI, VR2, and TR2. K9 guarantees a minimum dwell time (in this case approximately 2 ms ); as will be seen later this corresponds to maximum lamp intensity.

This resistor can be safely reduced to 22 k ! if absolute maximum brightness is required, but if this
is done the circuit begins to operate on the edge of stability. In actual fact, very little increase of light output was apparent by firing earlier in the cycle than 36 degrees which is what 2 ms represents.

The maximum dwell time is set by VR1. This is necessary to prevent the possibility of the monostable "hanging on" into the next mains half-cycle. The effect of deliberately causing this to happen will be described during the setting up procedure. Maximum dwell time should be approximately 9 ms for stability-this also allows for variations in mains frequency.

Having set the minimum and maximum dwell times, intermediate periods can be set by adjusting VR2 (the front panel control) or by causing TR2 to draw current. Voltage control of this dwell time is effected by drawing base current through TR2 by a voltage applied to the input of R6. It is important to note that the control voltage must be negative with respect to the positive rail as TR2 is a $p n p$ transistor.

No control is effected until the input voltage exceeds the emitter-base forward voltage drop $(500-600 \mathrm{mV})$. As the input voltage increases the collector current of TR2 increases in proportion and thus linearly reduces the dwell time of the monostable. See Fig. 4e and $4 f$.

As it is the dwell time which determines the position of the ultimate trigger pulse within the mains half-cycle, it is the negative going excursion of the collector of TR4 that is used. This is differentiated by C6 and R13 before being applied to TR5 which provides the trigger pulse drive into the isolating transformer T2.

The output of T2 is directly connected across the cathode and gate of the thyristor or triac. The amount of gate current to the thyristor is determined by the tuned circuit C7 and T2 primary. If this gate current is insufficient for the device used C7 can be


Fig. 5. Circuit diagram of the monostable timing and trigger for one channel


Fig. 6. Simple thyristor matrix of two by two. It is necessary to include the ballast loads (RI to R4 shown dotted) in the form of 15 watt lamps. These will have a higher resistance than the lamps at the matrix nodes, but still low enough to provide at least 20 mA holding current for the thyristors. Each lamp node should not be less than 40 watts to minimise interaction


Fig. 7. A complete four-by-four matrix where symbols A to P represent the lamp nodes ( 40 watts each), symbols RI to R8 represent the ballast loads ( 15 watt bulbs), DII to D26 steering diodes to avoid interaction are rated at 600 V IA for each lamp node. Thyristors for channels 1 to 8 must each be rated at four times the current through each node.
increased to a value up to $0 \cdot 2 \ell \mathrm{~F}$. Trigger current for the thyristors or triacs is not greater than 30 mA $3 V$. Polarity of the output of $T 2$ is not important owing to differentiation of the waveform.

## TRIAC AND THYRISTOR MATRIX

It was mentioned earlier that a novel type of output was available from the controller, and it is worth discussing at this point as it requires a slight variation in thyristor orientation. If it is desired, each control channel can be used independently of any other, thus one can control up to eight lamp circuits. If this is all that is required then the following details can be ignored and the circuits wired up exactly according to Fig. 5.

Provided one is prepared to use thyristors, it is possible to obtain up to 16 lamp control channels from the eight basic trigger circuits. This is done by matrixing four of the channels against the remaining four.

The principle of the matrix is shown in Fig. 6, which represents four lamp circuits controlled by four thyristors ( $\mathrm{x} 1, \mathrm{x} 2, \mathrm{yl}$, and y 2 ). One side of lamps $A$ and $B$ are commoned and taken to the cathode output of thyristor at y2; similarly one side of $C$ and $D$ is taken to yl. Conversely the free side of $A$ is commoned with $C$ and taken to xl ; similarly with $B$ and $D$ to $\times 2$.

Note, however, that the commoned sides of $A$ and $C$ with $B$ and $D$ go to the anode ends of thyristors $x 1$ and $\times 2$. The anodes of the thyristors on the $Y$ axis are both taken to one side of the mains (say "line") and the cathodes of those on the $X$ axis to "neutral". All the thyristors can be individually controlled by trigger pulses from the control channels.

If one ignores the fact that a thyristor needs a holding current to sustain conduction, one can simply say that if $y l$ and $x l$ are triggered, lamp $A$ will go on; $y 2$ with $x l$ and $x 2$ will light $A$ and $B$ and so on. In practice, however, this simple concept will not work unless trigger pulses arrive at the $x$ and $y$ thyristors simultaneously.

Assume that y 2 is triggered but neither x 1 or $x 2$; no current will flow through $y 2$ and hence it will immediately extinguish at the end of the trigger pulse. If a trigger pulse was to arrive at xl or x 2 later but within the same half-cycle, neither of these would hold on.

## HOLDING CURRENT

For the matrix to work we must provide some holding current when either axis switches. This holding current can be provided by the resistors shown dotted as R1 to R4 (Fig. 6). If either of the thyristors on the $Y$ axis are now triggered they will


Top view of the controller chassis showing the circuit boards and power unit
draw current through either R1 or R2. Likewise for devices on the $\mathbf{X}$ axis through R3 or R4.
The values of these resistors must be carefully chosen so that they pass sufficient holding current, but not sufficient current for any apparent illuminaltion of the main lamps A, B, C, and D, which are in effect in a complicated series parallel arrangement with the resistors. In operation the thyristors work by by-passing the resistors rather like toggle switches.
A few moments puzzling over a network analysis of the equivalent circuit under all combinations of switching will show that the problem is extremely complex. If the circuit was scaled up to a four-byfour matrix the problem could only be satisfactorily solved by computer.

Without going into the complicated mathematics it is sufficient to say that the problem can be solved in two ways:

1. The holding current resistors should be of very high resistance compared with the lamps, or
2. We allow current only to flow in one direction through the main lamps by using "steering diodes.

The author has used both methods and quite definitely the diode solution, al though more expensive, is by far the best.
Even with diodes one still has to provide holding current and the simplest solution to obtaining resistors of sufficient power rating is to use low power mains rated lamps (these can ultimately be incorporated as part of the display). This holding current is provided by 15 W bulbs which allow a reasonable matrix effect if the main display lamps are not less than 40 W each.
If diodes (of sufficient voltage and current rating) are also used they should be connected in series with each main lamp in the same direction as the thyristors.

## LAMP LOADS

Using 40W bulbs in the main display, a perfect matrix display, with no parasitic interaction, is obtained. Fig. 7 shows the complete circuitry for the four-by-four matrix using diodes as recommended.

It is important to note that each thyristor on each axis must be capable of handling the load of all four lamps to which it is commoned. In this article we shall be considering 1A thyristors without heat sinks, thus the maximum current that may be drawn by each lamp node is 250 mA (i.e. approximately 60 W ). This can easily be extended by using higher current rated thyristors mounted on heat sinks; however, for domestic use 16 lamps of 60 W each are more than adequate.

No advantage is obtained by using triacs in the matrix when diodes are in use. They will, of course, increase the available light in the simple resistor only matrix but will exaggerate the interaction of current paths.

Next month: construction of the lamp control unit
P.E. AURORA AUDIO BAND SPLITTING FILTER UNIT FOR OPERATION WITH SOUND WILL BE DESCRIBED IN PART THREE



## by C. R. Bradley

There are many cases where it would be convenient to be able to switch equipment on and off by touch alone. The device described here enables any equipment to be switched merely by momentary hand contact with the sensitive touch plate.

Some advantages and possible applications for the switch are as follows. The sensitive plate can be made large and therefore easier to find and operate than a conventional toggle switch. Hence the touch switch could be useful for operation in darkness, or operation by blind or otherwise disabled persons.

It can also serve as a cut out switch on potentially dangerous machinery as operation is quicker than either a toggle or push button switch. In some cases the touch plate could be an insulated metal part of the machine which is unsafe to touch; any bodily contact with the part would cause the machine to stop.
A further advantage of the touch switch is that little or no vibration need be caused by its operation. The author has found it convenient to mount a touch switch on his photographic enlarger. The large touch plate is easily found in the dark and if it is touched lightly there are no undesirable vibrations of the enlarger. There are also many applications for the touch switch in burglar alarm devices.


Fig. 1. Circuit diagram of Touch Switch

## F.E.T. INPUT

The circuit of the touch switch is shown in Fig. 1. A field effect transistor, TR1, is used at the input to provide a very high input impedance, to the noise voltages developed across the resistor chain R1-R6 through contact with the touch plate.

The source, gate and drain electrodes of the $n$-channel f.e.t. are closely analogous to the cathode, grid and anode of the triode valve. The voltage drop across source load R2 biases the gate negative with respect to the source. With the values shown, the f.e.t. is biased close to pinch-off, corresponding to valve cut-off.

## TOGGLE ACTION

On touching the touch plate, the stray noise introduced raises the mean drain/source current and the potential across Cl rises. When the touch is removed the potential falls. This negative swing is passed by C3 and C5 to cause the bistable circuit of TR2 and TR3 to change state.

When TR2 is conducting, its collector is close to earth potential and TR3 is biased off via VR1. TR2 is held in conduction by current through R10 and therefore this state is stable. The small current through the relay is insufficient to energise it.

If now a negative pulse is fed to TR2 base via C3 and D1, TR2 turns off. Its collector goes positive and TR3 is turned on via VR1. The collector of TR 3 swings towards earth so that TR2 is no longer biased on. The circuit is now in its other stable state where there is sufficient current in the relay to energise it.

A negative pulse fed to TR3 base via C5 and D2 causes the circuit to change state again. The relay contacts switch the power to the equipment to be controlled. Thus the switch provides a touchon, touch-off operation.

## COMPONENTS . . .

```
Resistors
    RI-R6 IOM\Omega (6 off)
    R7 6.8k\Omega
    R8 10k\Omega
    R9 470k\Omega
    RIO IM\Omega
    RII 470k\Omega
    All }\pm10% \frac{1}{2}\mathrm{ watt carbon
Capacitors
    Cl 64\muF elect. 40V
        0.1 HF polyester
        l }\mu\textrm{F}\mathrm{ polyester
        0.01 \muF ceramic
        I MF polyester
Transistors
    TRI 2N3819
        TR2-TR3 ZTX302 (2 off)
Diodes
        DI-D3 OA8I (3 off)
Relay
        RLA 700\Omega, 2; pole C/O relay type 43
                            (Radiospares) or type MH2 (Omron)
```


## Miscellaneous

```
BYI-9V batteries ( 3 off), Veroboard \(2 \frac{1}{2}\) in \(\times 3\) in 0.1 in matrix, 6 in \(\times 4\) in \(\times 2 \frac{1}{2}\) in aluminium.
```



As TR3 has an inductive load, its turn on time has to be speeded up by the addition of C4. It is also protected by diode D3 against transient voltages induced in the relay.

The a.c. gain of TR2 is reduced by C2 to prevent relay chatter.

The times taken for C3 and C5 to charge through R9 and R11 respectively affect the rate at which the bistable states can be changed and these time constants are made large to ensure stable operation.

## RESISTOR CHAIN

The large total value of the resistor chain R1-R6 was found to give good sensitivity. It is obtained by connecting six, 10 megohm carbon resistors in series and arranging for them to be self supporting to avoid leakage problems.

Higher resistance values will provide a higher input impedance and hence more sensitivity but there is a diminishing return as the f.e.t. gate impedance becomes more significant in comparison. If the resistance of $R 1$ is made infinite, or in other words R1 is just an open circuit, the input impedance is so high that the f.e.t. responds to static charges.

Electrolytic capacitors cannot be used for C3 or C5 as these capacitors receive charges of opposite polarity in the two bistable states. Small paper or polyester types are suitable.

## CONSTRUCTION

The circuit components are arranged on a small piece of Veroboard (Fig. 2) mounted inside an aluminium chassis as shown in Fig. 3. The chassis is connected to battery negative to provide screening for the circuit. Layout is not critical and the unit can be made smaller provided it is fully screened.

If mains equipment is to be controlled a piece of metal, bolted to the chassis, should be used to screen the relay contacts from the rest of the circuit.

The supply is made up of three 9 V batteries connected in series to give 27 V ; the circuit will work well on any voltage between 18 V and 30 V .

A tin lid can be used for the touch plate. This is supported above the chassis by a short piece of Bakelite tube as it is important to maintain a high insulation and a low capacity between the touch plate and the chassis.


Fig. 2. Assembly and wiring details of topside and underside of Veroboard sub-assembly. Resistor R8 is shown on the underside, broken to reveal the connection ot hole 6 L for RII


Fig. 3. Chassis mounted components and Veroboard wiring detalls. The precise details of connecting the relay contacts will depend on the circuit application


For a more robust support Bakelite sheet can be used with Araldite for chassis fixing.

## SETTING UP

When the wiring is complete connect the supply. Set VR1 to mid-position and switch on. The bistable will immediately go into one of its two stable states and the relay may energise.

Touch the touch plate to see if this will trigger the bistable. VR1 must be carefully adjusted to give proper action and equal "on" and "off" sensitivity and stability. If the resistance is set too high, TR3 will not conduct hard enough to keep the relay energised.
As VR1 resistance is reduced, a point may be reached where touching the touch plate causes the relay to chatter. Reducing the resistance a little more will give the proper operating point. If the resistance is too low the relay will remain permanently energised; if this should happen for all settings of VR1 it may be necessary to reduce R 5 to $820 \mathrm{k} \Omega$ or $680 \mathrm{k} \Omega$.

If the circuit fails to work, the f.e.t. stage can be checked by connecting a voltmeter across C1. Touching the plate should cause an increase in deflection.

The bistable can be checked by connecting a lead to battery negative and touching it to the base of whichever of TR2 and TR3 is conducting. This should cause the bistable to change state.

## SENSITIVITY

When the switch is used in a building, it responds to the mains radiation transferred by bodily contact with the touch plate. When used away from mains wiring it responds to radio frequencies and is somewhat less sensitive. It will not work in a completely screened room or react to the touch of a person who is well "earthed".

If C 2 is reduced in value or removed, the touch switch becomes slightly more sensitive and mere body proximity may be enough to cause switching. But under these conditions the setting of VR1 is extremely critical and the switch is less stable. $\star$
where $I_{\mathrm{Dp}}=$ maximum diode current
$V_{\text {in }}=$ supply voltage
$V_{\mathrm{Dp}}=$ Zener voltage
$R_{\mathrm{S}}=$ series resistance in ohms
Assuming an integrated circuit supply having an input voltage of 12 V and an output rating of 5.1 V at 1 A , the resistor $R_{\mathrm{s}}$ would normally have a value of 4 ohms. Consequently the $6 \cdot 2 \mathrm{~V}$ protection Zener should be capable of carrying 1.5 A continuously, and therefore a $10 \mathrm{~W}, 6 \cdot 2 \mathrm{~V}$ Zener diode mounted on a heatsink would be required.

It should be noted that the power rating of the series resistor must be capable of 9 W continuous dissipation.

From this it can be seen that the protection Zener diode must be capable of holding and dissipating the full output power of the supply, therefore it is only suitable for low power stabilised supplies.

As an example a 24 V d.c. supply capable of delivering 1A would require a protection diode of 26 to 30 W rating and clearly this is impractical. For higher power circuits, therefore, crowbar protection circuits are utilised.

## CROWBAR PROTECTION

Crowbar protection circuits operate by effectively causing a short circuit across the supply until the line fuse ruptures. Unlike Zener protection where an intermittent fault would result in a return to normal working after the fault cleared, crowbar circuits positively isolate the faulty power supply.

This can be an advantage in very complex systems. Any failure condition can be used to operate the crowbar circuit and these include overvoltage, overcurrent and overpower.


Fig. 2. Overvaltage crowbar protection

$$
I_{\mathrm{Dp}}=\frac{V_{\mathrm{in}}-V_{\mathrm{Dp}}}{R_{\mathrm{S}}}
$$

## OVERVOLTAGE CROWBAR

In Fig. 2 is shown a typical overvoltage crowbar system operating in conjunction with a high power series stabiliser.

Any overvoltage at the output causes the sensing Zener diode $D_{\mathrm{p}}$, to conduct, so passing current to the thyristor gate. The thyristor SCR1 switches on and causes a heavy current to flow through the fuse until it ruptures.

Since the circuit operates only for a very short period the Zener diode can be of 100 mW rating as can the thyristor gate resistor.

The thyristor is chosen for its peak transient current rating which can be 25 A to 100 A for a TO-5 case thyristor. The series resistor $R_{\mathrm{S}}$ is a low value wirewound resistor which simply limits the peak transient current.

Whilst an actual overvoltage condition must occur before the crowbar circuit operates, the overvoltage acts for a very short period.

Since the turn-on time of the thyristor is 10 to $20 \mu \mathrm{~s}$ and following this a large current flows through the fuse, the supply voltage reduces almost immediately. Consequently the circuitry operated from the power supply receives an overvoltage transient of only 10 to $20 \mu$ s duration which is usually insufficient time to cause circuit failure.

Because the ratings are based on transient effects, low cost components can be used.

## OVERCURRENT CROWBAR CIRCUIT

One form of overcurrent crowbar circuit is illustrated in Fig. 3 and it can be seen that a certain amount of increased complexity, and therefore expense, is involved.


The current level is sensed by resistor $R_{\mathrm{c}}$ which is chosen to give approximately 0.5 to 0.75 voltage drop at the fusing current. Generally the fusing current is chosen to be 150 to 200 per cent of full load current. When the current reaches this level the transistor conducts and operates the crowbar thyristor.

The resistor capacitor combination $\mathrm{R} 4, \mathrm{R} 3$, and Cl are incorporated to limit the speed of response of the circuit. This is a vital precaution since the capacitors in the stabiliser and following circuitry usually require a heavy switch-on charging current, consequently the time constant $C_{1} R_{4}$ must be longer than any switch-on surge current periods.

Typical component values using a transistor series stabiliser are $\mathrm{R} 4=680 \Omega, \mathrm{R} 3=1.8 \mathrm{k} \Omega, \mathrm{Cl}=10 \mu \mathrm{~F}$.

## COMPARISON WITH A FUSE

With the increased complexity and difficulties inherent in the design of overcurrent trip circuits, the usefulness of this type of circuit is doubtful. For the vast majority of applications the simple fuse is adequate. However, occasionally this form of circuit is necessary for the protection of complex power equipment.

The main advantages over the simple fuse are a more definite fuse current, increased speed of response and greater reliability.

Reliability is perhaps the most important aspect, since the fuse incorporated with the crowbar circuit can be two or three times the rated current. This increased rating could well increase fuse life by three to ten times above the 1,000 hours usually quoted.

## OVERPOWER CROWBAR CIRCUIT

The overpower crowbar circuit is seldom employed but can have very useful applications. The simplest form of circuit is given in Fig. 4 and consists of a thermistor for temperature sensing together with the thyristor crowbar.

In this example, the directly heated bead type thermistor is located on the surface of the series transistor of the stabiliser. Any excess power dissipation in the series transistor, such as produced by a short circuit, would result in overheating and consequent reduction in thermistor resistance. After a thermal delay period the minimum gate voltage will be exceeded and the thyristor triggers.

Since the body of the thermistor is isolated, any critical or expensive component in any part of the circuit can be monitored. Therefore this form of protection is extremely versatile.

Unfortunately, this form of protection requires a fairly large temperature change for reliable operation and is suitable only for non-critical operation. For more critical operation a single transistor comparator circuit can be used to give an accuracy of temperature measurement to $\pm 5$ degrees Centigrade.

## APPLICATIONS

The Zener diode protection circuits are only suitable for low power supplies, although they are useful for high current low voltage integrated circuit power supplies.

The thyristor crowbar circuits can be used for any size power supply, and it can be arranged for any type of fault condition to fire the thyristor. The crowbar circuits given can be combined to give a comprehensive protection device using a single thyristor, sensing Zener diode, thermistor and transistor. All the circuits are separate to the basic power supply and modifications to this are not required.

# mp <br> R <br> PLACE 

Items mentioned in this feature are usually available from electronic equipment and component retailers advertising in this magazine. However, where a full address is given, enquiries and orders should then be made direct to the firm concerned.

## STEREO TAPE CARTRIDGE

Offering 40 minutes and 80 min utes recording time, compared with the 30 and 60 minute version currently available, is the main feature of the new Scotch 8-track tape cartridges. type S-8TR-40 and S-8TR-80, from the 3M Company.

The Scotch 8 -track cartridges may be used in any cartridge system having recording facilities and may, of course, be played back on any 8track stereo equipment. The extra 10 minutes on the S-8TR-40 permits the complete recording of an average 12 in . LP record.

Recommended retail prices are fl 50 for the 40 minute cartridge. and $£ 1.80$ for the 80 minute version.

## MOULDED TRACK <br> POTENTIOMETER

Potentionmeters, types T and TS. of all-moulded construction, including the bush and fixing nut, are announced by Plessey.

The type TS is identical to the Type $T$ except that it incorporates a single-pole switch which is suitable for low voltage battery circuits.


Scotch 8-track stereo tope cortridge from the 3M Company

The case is in two halves and is ultrasonically welded together to provide a completely insulated potentiometer.
These potentiometers are particularly suitable for portable transistor receivers and other equipment where a miniature moulded track potentiometer is required.

Full details and technical specifications can be obtained from Painton Electronic Components. Kingsthorpe. Northampton, NN2 6NA.


Plessey type TS and $T$ miniature moulded potentiometers

## FLASH TUBE

A new photographic flash tube, the Type CD13, has been introduced by the Electronic \& Display Equipment Division of Ferranti as an addition to its range of tubes for photographic and similar applications.

A high intensity xenon-filled flash tube for electronic flash equipment, the CD13 produces a white light which is a good match to daylight and is suitable for "daylight" colour films. This device is a straight tube 210 mm long.

Operating voltage of the tube ranges between a minimum 400 V and a maximum $1,000 \mathrm{~V}$, and the typical operating level is 900 V . The CD13 is not polarised and the charging voltage and discharge capacitor may be connected across the leads without regard to polarity.

Details of price and local stockists can be obtained from Ferranti Ltd., Electronic and Display Equipment Division, Gem Mill, Chadderton, Oldham, Lancashire.

## CIRCUIT BOARDS

Quality printed circuit boards are now available for the circuits shown in the Mullard book "Transistor Audio and Radio Circuits ". The boards manufactured by Bribond Printed Circuits Limited, Terminus Road, Chichester, Sussex, are made to the same standards as their industrial boards.

The boards are manufactured from high electrical grade s.r.b.p. laminate clad with 0.0015 in copper. The copper tracks are tinned to aid soldering and give protection against oxydisation. To aid construction, the
component identification is printed on the reverse in white.

At the moment the following circuits are available:-
10W high quality aüdio amplifier (p. 102) 66p

25W high quality audio amplifier
(p. 106) 70p

10/25W high quality audio preamplifier (p. 108) 73p
10W audio amplifier (p. 39) 66p
10 W audio preamplifier (p. 42) $69 \frac{1}{2} \mathrm{p}$
Price each including postage and packing.

## LITERATURE

The new component catalogue from A. Marshall \& Son (London) Ltd, is now available to readers. The catalogue lists many new items but probably the most interesting, to our readers, is the section on integrated circuits. This section contains one of the largest selections of I.C.'s available to the amateur we have seen. Apart from the English manufacturers there is a large range from American firms.

Request for copies should be addressed to, A. Marshall \& Son (London) Ltd., 28 Cricklewood Broadway, London, N.W.2.

All the new editions of the component catalogues from Henry's Radio, Home Radio (components), G. W. Smith \& Co. (Radio), and LST Components are up to their usual high standard and make a useful reference for the workshop.
Of particular interest to designers is a revised designers' guide to mercury and alkaline manganese primary power systems published by Mallory Batteries.

In addition to describing the two primary cell systems, the guide explains their advantages under widely differing environmental conditions.

It provides detailed specifications of over 100 different cells with the object of giving designers such basic information as capacity, nominal voltage and dimensions.

The designers' guide is also available in French and German and full details can be obtained from Mallory Batteries Ltd., Gatwick Road, Crawley, Sussex.

Containing more than 70 new products, ranging from an 8 -track stereo cartridge player for cars to a multi-meter for test engineers, Eagle International's new 45-page catalogue is now available from Eagle International, Coptic Street, London. WCIA LNR, price 20p.

Divided into sections on hi fi equipment, hi fi accessories and peripherals, radio and tape equipment, office intercoms, public address, test equipment, electronics and accessories, the catalogue carries illustrations, detailed specifications and prices of over 400 products.

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THERE are many ways of making an ohmmeter circuit; the most popular circuits can be reduced to either of two basic types which, for convenience, we will designate A and B .

In the A-type circuit (Fig. 1), a battery is connected in series with a fixed resistor ( R 1 ), a variable resistor (VR1), and the indicating meter (M1). $R_{\mathrm{m}}$ is the internal resistance of the meter and $R_{1}$, the total resistance in the circuit, is equal to $R_{\mathrm{I}}+R_{\mathrm{VR}}+R_{\mathrm{m}}$.

## SIMPLE MEASUREMENT

The unknown resistor ( $R x$ ) is connected between the two ohmmeter terminals $X$ and $Y$, which places it in series with the rest of the circuit. To determine the value of $R x$, the $X$ and $Y$ terminals are first shorted together (so as to simulate $\mathrm{Rx}=\mathbf{0}$ ohms); VR is then carefully adjusted so that M1 just indicates full-scaledeflection (f.s.d.). This procedure is called zeroing the ohmmeter, and is necessary to compensate for ageing of the battery.

The short-circuit between X and Y is then replaced with $R x$ and the meter indication, which will now be less than f.s.d., gives an indication of the value of $R x$; the greater the value of $R x$, the smaller the deflection.

## CALIBRATION

To illustrate how this circuit works, let the battery voltage $V_{b}$ equal 1.5 V and let the f.s.d. of Ml equal $50 \mu \mathrm{~A}$. When the ohmmeter is zeroed, VR1 must be adjusted so that the meter current ( $I_{\mathrm{m}}$ ) equals $50 \mu \mathrm{~A}$, which means that $R_{\mathrm{t}}=\frac{1 \cdot 5 \mathrm{~V}}{50 \mu \mathrm{~A}}=30 \mathrm{k} \Omega$. Leaving $R_{\mathrm{t}}$ set at $30 \mathrm{k} \Omega$, now connect to the $X$ and $Y$ terminals, an unknown resistor ( Rx ) of such a value that $I_{\mathrm{m}}$ is reduced to $25 \mu \mathrm{~A}$ (mid-scale). From Ohms law,

$$
\begin{align*}
& I_{\mathrm{m}}=\frac{V_{\mathrm{b}}}{R_{\mathrm{x}}+R_{\mathrm{t}}}  \tag{1}\\
& R_{\mathrm{x}}=\frac{V_{\mathrm{b}}}{I_{\mathrm{m}}}-R_{\mathrm{t}} \tag{2}
\end{align*}
$$

$R_{\mathrm{x}}=\frac{1.5}{25 \times 10^{-6}}-30 \times 10^{3}=30,000$ ohms which is the same as $R_{\mathrm{t}}$.

This is the first important point to notice about the A-type circuit; the mid-scale resistance vaiue is equal to the value of $R_{\mathrm{t}}$ corresponding to $R_{\mathrm{x}}=$ zero.

Knowing that $V_{\mathrm{b}}$ equals 1.5 V , and that $R_{\mathrm{t}}$ equals $30 \mathrm{k} \Omega$ for $I_{\mathrm{m}}=50 \mu \mathrm{~A}\left(R_{\mathrm{x}}=0\right)$, a table of $R_{\mathrm{x}}$ for corresponding values of $I_{\mathrm{m}}$ can be compiled by substituting values of $R_{\mathrm{x}}$ in equation 1 above (Table 1 ).

From this table a suitable ohms scale may be produced, which can then be marked on the meter dial face; this is illustrated in Fig. 2, for a few values of $\boldsymbol{R}_{\mathrm{x}}$.

TABLE I

| Resistor | Meter |
| :---: | :---: |
| on test | current |
| $R_{\mathrm{x}}$ | $(\mu \mathrm{A})$ |
| (ohms) | $50($ f.s.d. $)$ |
| 0 | 49.8 |
| 100 | 48.4 |
| 1 k | 37.5 |
| 10 k | 25 |
| 30 k | 11.52 |
| 100 k | 1.5 |
| 1 M | 0 |



Fig. I. "A"-type circuit where the battery, meter and variable resistor are all in series


Fig. 2. Typical dial calibration for the example described with Table 1

## SCALE CRAMPING

Note that zero ohms ( $I_{\mathrm{m}}=50 \mu \mathrm{~A}$ ) occurs at the right-hand end of the scale, and that infinite resistance ( $I_{\mathrm{m}}=0 \mu \mathrm{~A}$ ) corresponding to $R_{\mathrm{x}}=$ open-circuit, occurs at the left-hand end.

The scale is also non-linear, following a line of $1 / R$. It appears severely cramped at the high-resistance end and open at the low resistance end. In fact, if we assume $1 \mu \mathrm{~A}$ to be the smallest discernible deflection of the meter pointer (corresponding to 2 per cent of f.s.d.), then we can say that the largest measurable resistance with this particular circuit is about $1.5 \mathrm{M} \Omega$, using equation 2. Even so, cramping is so severe in this region of the scale that anything greater than about $1 \mathrm{M} \Omega$ is almost unmeasurable.

To measure greater resistance values with this particular circuit (without changing to a more sensitive meter), it is necessary to increase the value of $V_{\mathrm{b}}$.

## INCREASING RANGE

Increasing $V_{b}$ from 1.5 V to 15 V increases the measurable resistance by ten times, and also the value of $R_{t}$ required for the zero-ohms setting from $30 \mathrm{k} \Omega$ to $300 \mathrm{k} \Omega$, as is the mid-scale resistance indication.

The advantage of providing a tenfold increase in the value of $V_{b}$ means that a single ohms scale can be used for a two-range ohmmeter, the readings corresponding to the higher range being multiplied by ten by the user. This is common practice; typical basic two-range ohmmeter circuits might look like those shown in Fig. 3.

In Fig. 3a, separate VR controls are provided, whereas in Fig. 3b a single VR control is shared by the two ranges. The advantage of having separate controls means that once the two ranges have been zeroed properly it is possible to change from one range to the

other without having to re-zero each time. The only disadvantages of having two controls are additional expense and greater panel space needed to accommodate them.

In the case of one control types of circuit, it is usually fairly coarse in operation, i.e. small adjustments bring about comparatively large changes in the meter indication, which makes zeroing rather difficult.

We have recently seen that the required value of $R_{t}$ for the oHms $\times 1$ range ( $V_{\mathrm{b}}=1.5 \mathrm{~V}$ ) is $30 \mathrm{k} \Omega$, and that for the $\Omega \times 10$ range ( $V_{b}=15 \mathrm{~V}$ ) it is $300 \mathrm{k} \Omega$. The value of VR1 in Fig. 3 b should be made as small as possible for the OHMS $\times 10$ range, so that it is no larger than absolutely necessary when it is used for the oHMs $\times 1$ range (a resistance value which is small compared with $300 \mathrm{k} \Omega$ is likely to be large when compared with $30 \mathrm{k} \Omega$ ).

## BATTERY AGEING

The batteries used in most ohmmeter circuits are of the carbon-zinc type, a type which is notorious for the variations which occur in its terminal p.d. throughout its life. Because of this, when a new battery is purchased, its terminal p.d. is quite likely to be higher than its nominal voltage, even when delivering a small load current.

In time, however, even if not used, its p.d. will fall and its internal resistance will increase considerablyso much so that it will be unable to deliver the required voltage for the circuit. When it has reached this state the battery is considered as being fully discharged and should be replaced.

## AGEING COMPENSATION

In view of this, the resistance of VRI must be sufficient to compensate for changes in $V_{b}$ ranging from about 13 V to 16 V on the ohms $\times 10$ range, and from about 1.3 V to 1.6 V on the $\mathrm{oHms} \times 1$ range.

Taking the oHMS $\times 10$ range first; when $V_{b}$ is 16 V , the value of $R_{\mathrm{t}}$ required to limit $I_{\mathrm{m}}$ to f.s.d. $(50 \mu \mathrm{~A})$ when zeroing the ohmmeter is

$$
R_{\mathrm{t}(\max )}=\frac{16 \mathrm{~V}}{50 \mu \mathrm{~A}}=320 \mathrm{k} \Omega
$$

Similarly, when $V_{\mathrm{b}}=13 \mathrm{~V}$

$$
R_{\mathrm{t}(\min )}=\frac{13 \mathrm{~V}}{50 \mu \mathrm{~A}}=260 \mathrm{k} \Omega
$$

It is the difference between these two required values of $R_{\mathrm{t}}$ which must be compensated for by VR1; the value of VR1 should therefore be $60 \mathrm{k} \Omega$.

Since this is not a standard value for a potentiometer, we must either accept a value of $50 \mathrm{k} \Omega$, which means we won't be able to compensate completely for all changes in $V_{\mathrm{b}}$, or one of $100 \mathrm{k} \Omega$, which would be much too coarse when used on the ohms $\times 1$ range ( $R_{\mathrm{t}}$ for the oнms $\times 1$ range is only $30 \mathrm{k} \Omega$ ). The sensible thing to do then is to select the $50 \mathrm{k} \Omega$ value and to accept the limitation on $V_{\mathrm{b}}$ compensation.

## RANGE RESISTOR

The next thing to do is select suitable values for $\mathbf{R} 1$ and R2. Now, since $R_{t(\max )}$ for the ohms $\times 10$ range is $320 \mathrm{k} \Omega$, and VR1 is $50 \mathrm{k} \Omega$, then $\mathrm{R} 2=(320-50) \mathrm{k} \Omega=$ $270 \mathrm{k} \Omega$-which happens to be a preferred value resistor.

Unfortunately, we run into another problem here, and that is the selection tolerance of R2. For cheapness a $\pm 20 \%$ type could be used, but the value of VR1 (which itself will have a tolerance of $\pm 10 \%$ ) would have to be large enough to compensate for tolerance differences in $\mathbf{R} 2( \pm 20 \%$ of $270 \mathrm{k} \Omega= \pm 54 \mathrm{k} \Omega$ ), as well as for changes in $V_{\mathrm{b}_{2}}$.

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To be able to do this, VR1 would have to be made $100 \mathrm{k} \Omega$, which is unacceptably large for the oHms $\times 1$ range. The simplest solution would be to use a closer tolerance resistor for R 2 and accept a reduction in the compensating ability of VRI. Ideally, this should be of $\pm 1 \%$ tolerance before an acceptable result is obtained.

## OHMS $\times I$ RANGE RESISTOR

Having settled on the value of R2 in Fig. 3b, we must now turn our attention to the oHMS $\times 1$ range and determine the value of R1.

Since $V_{\mathrm{b}_{1}}$ is one-tenth of $V_{\mathrm{b}_{2}}$, then the corresponding values of $R_{\mathrm{t}(\max )}$ and $R_{\mathrm{t}(\mathrm{min})}$ for maximum and minimum values of $\mathrm{V}_{\mathrm{b}_{1}}$ will be one-tenth of those values determined for $R_{\mathrm{t}(\max )}$ and $R_{\mathrm{t}(\min )}$ for $V_{\mathrm{b}_{2}}$. For the ohms $\times 1$ range then, $R_{\mathrm{t}(\max )}=32 \mathrm{k} \Omega$ and $R_{\mathrm{t}(\min )}=$ $26 \mathrm{k} \Omega$.

This means that VR1 for this range, should ideally be equal to the difference between these two values, i.e. $6 \mathrm{k} \Omega$. However, VR1 has already been selected as being $50 \mathrm{k} \Omega$ which is nearly ten times greater than $6 \mathrm{k} \Omega$ and VRI is already greater than the largest value ever required for R1.

In this case we don't need RI at all since VR1 ( $50 \mathrm{k} \Omega$ ) is more than big enough to cope with all required values of $R_{\mathrm{t}}$. However, if R 1 is dispensed with altogether, there would be no built-in protection for the meter if VRI should inadvertently be set to zero. By insertion of a large value for R1, the operation of VRI is even coarser than it is already (it is almost ten times greater than it need be).

Resistor R1 must be made large enough to provide a substantial degree of overload protection for the meter, and yet small enough to have little effect on the sensitivity of VR1.

If the meter current is limited to a value equal to ten times the f.s.d. current (most meters will just about stand a $10: 1$ instantaneous overload) then the overload current will be $500 \mu \mathrm{~A}$ and the corresponding value for $R_{\mathrm{t}}$ (assuming VR1 is set to zero, and $\mathrm{V}_{\mathrm{b}_{1}}$ is at its highest value of 1.6 V ) will be equal to $\frac{1.6 \mathrm{~V}}{500 \mu \mathrm{~A}}=3.2 \mathrm{k} \Omega$. Then, $\quad R_{1}=R_{\mathrm{l}}-R_{\mathrm{m}}=1.7 \mathrm{k} \Omega$. The nearest preferred value is $1.8 \mathrm{k} \Omega$.

## INDICATION ACCURACY

Before leaving the A-type ohmmeter circuit, it is important to note a very serious drawback concerning its indication accuracy. The validity of the mid-scale indications (the oHms $\times 1$ range is $30 \mathrm{k} \Omega$, and on the ofms $\times 10$ range it is $300 \mathrm{k} \Omega$ ) only applies when the battery voltages are 1.5 V and 15 V , respectively. See what happens to the indications when the battery voltages are first high, and then low; this need only be done for one ohmmeter range because the overall effect will be the same for both ranges.

Taking the oнms $\times 1$ range, and a $V_{b(\min )}$ value of $1 \cdot 3 \mathrm{~V}$, the value of $R_{\mathrm{t}}$ required to achieve f.s.d. $(50 \mu \mathrm{~A})$ is $26 \mathrm{k} \Omega$. The value of VRI will be adjusted during the zeroing procedure so that it equals $26 \mathrm{k} \Omega$.

From earlier deductions, the value of $R_{\mathrm{t}}$ required to bring about f.s.d., is also equal to the value of an external resistor ( $R_{\mathrm{x}}$ ) required to bring about halff.s.d. $(25 \mu \mathrm{~A})$. Consequently, the mid-scale indication of the oHms $\times 1$ range when $V_{b}$ is 1.3 V (instead of $1 \cdot 5 \mathrm{~V}$ ) is $26 \mathrm{k} \Omega$, instead of $30 \mathrm{k} \Omega$, i.e. $4 \mathrm{k} \Omega$ below normal. This represents an indication error of about - $13 \%$, which is almost the same as the corresponding reduction in the value of $V_{\mathrm{b}}$.

For a $V_{b(\max )}$ value of 1.6 V (about $7 \%$ above the 1.5 V normal value), the indication inaccuracy will be about $+7 \%$.

From these calculations we may deduce that the indication accuracy of the A-type ohmmeter circuit (quoted at mid-scale) is correct only when $V_{b}$ is equal to 1.5 V , and that the inaccuracy of this indication will vary from about $+7 \%$ when the battery is new, to about $-13 \%$ when it is ready for replacement. These facts are worth knowing, especially when using the ohmmeter to select a close tolerance resistor.

This completes the examination of the A-type ohmmeter. The reasons for going into its circuit in such detail were to illustrate the difficulties in reaching a suitable compromise for the component values, and to highlight its undesirable indication inaccuracies.

## PARALLEL POTENTIOMETER OHMMETER CIRCUIT

The B-type of circuit (Fig. 4) is basically very similar to the A-type circuit shown in Fig. 1, except that the variable resistor VR1 is connected in parallel with the meter (M1) instead of in series with it. The zeroing procedure is exactly the same except that, in this case, the meter current ( $I_{\mathrm{m}}$ ) is adjusted to f.s.d. by shunting the excess current ( $I_{\mathrm{s}}$ ) through VR1.

The total circuit current ( $I_{\mathrm{t}}$ ) is equal to the sum of $I_{\mathrm{s}}$ and $I_{\mathrm{m}}\left(I_{\mathrm{t}}=I_{\mathrm{s}}+I_{\mathrm{m}}\right)$, and is therefore greater than the corresponding value of $I_{t}$ for the A-type circuit in which $I_{\mathrm{t}}$ was always equal to $I_{\mathrm{m}}$. This type of circuit therefore consumes more power than the previous type.
The B-type circuit, for the same number of components, is much more flexible than the A-type and the zeroing control VR1 is much smoother in operation. The reason for this, as you will see, is that almost any value can be chosen for VR1, which means that it may

be used to determine the overall resistance range of the ohmmeter; in addition to its normal role of compensating for changes in $V_{b}$.

## BATTERY V COMPENSATION

Let us first consider the fundamental requirement of compensating for a change in $V_{b}$, assuming a nominal value of 15 V for $V_{\mathrm{b}}$ and a mid-scale resistance indication of $300 \mathrm{k} \Omega$ (the same as the corresponding indication for the A-type circuit).

Since the battery voltage $V_{\mathrm{b}}$ is likely to change from about 13 V (for old battery) to about 16 V when renewed, $I_{\mathrm{m}}$ will increase from $50 \mu \mathrm{~A}(13 \mathrm{~V} / 260 \mathrm{k} \Omega)$ to $61 \cdot 5 \mu \mathrm{~A}$ $(16 \mathrm{~V} / 260 \mathrm{k} \Omega)$. In order to compensate for this change in $I \mathrm{~m}$, VRI must be set to such a value that it will bypass the excess $11 \cdot 5 \mu \mathrm{~A}$ at present flowing in $R_{\mathrm{m}}$.

The value of VR 1 should be $50 / 11 \cdot 5$ or approximately 4.33 times greater than the value of $R_{\mathrm{m}}$; VRI should therefore be $6.5 \mathrm{k} \Omega$. This is illustrated in Fig. 5.

What we have just done is to determine the minimum value that VR1 is ever required to have in order to compensate for the maximum likely value of $V_{\mathrm{b}}$. One obvious advantage with this type of circuit is that no matter how large $V_{\mathrm{b}}$ might be, the excess current can always be fully absorbed by VR 1 since its value can, if necessary, be reduced to zero-thereby bypassing all the current.

## VR UPPER LIMIT

There is no upper limit for the value of VRI since we have already shown that $I_{\mathrm{t}}$ can never exceed $61.5 \mu \mathrm{~A}$ (with RI $=260 \mathrm{k} \Omega$ ), and that setting VR1 to $6.5 \mathrm{k} \Omega$ can take care of that current which is in excess of the $50 \mu \mathrm{~A}$ required by the meter.

It is, however, necessary to employ a reasonably large value for VR1 so that when set to its maximum value its shunting effect on $R_{\mathrm{m}}$ is negligible. This is important in order to ensure that $50 \mu \mathrm{~A}$ f.s.d. is still possible when $V_{\mathrm{b}}$ is approaching its minimum value of 13V. If VRI is set to a maximum value of $10 \mathrm{k} \Omega$ (by using a $10 \mathrm{k} \Omega$ variable resistor), then $I_{\mathrm{m}}$ would equal $43 \cdot 5 \mu \mathrm{~A}$ when $V_{\mathrm{b}}=13 \mathrm{~V}$ and $6 \cdot 5 \mu \mathrm{~A}$ would flow in VR1, giving a total ( $I_{t}$ ) of $50 \mu \mathrm{~A}$.

This means that it would not be possible to obtain f.s.d. when $V_{\mathrm{b}}$ had fallen to 13 V . Looking at it another way, we can say that the minimum value of $V_{\mathrm{b}}$ which can be tolerated with a $10 \mathrm{k} \Omega$ value for VR1 is about 15 V . The circuit as it stands, therefore, isn't going to be very useful because the battery will need replacing as soon as its potential has fallen to 15 V ; a value which is only a little less than its value when new.

## COMPROMISE

The alternatives are to reduce the value of R 1 , or increase the value of VR1. If the value of $R 1$ is reduced, then the mid-scale indication of the ohmmeter will also be reduced. On the other hand, if VRI is increased then its rate of adjustment will be more coarse, making it difficult to zero the ohmmeter, particularly when the battery is new and a comparatively low-value setting is required for VRI.

The final choice for VR1 is a compromise between mid-scale resistance indication and ease of zeroing adjustment. A useful rule-of-thumb in selecting a value for VRI in this type of circuit is that its value should not exceed about ten times the value of $R_{\mathrm{m}}$ (the resistance of the meter). In the example we have just considered, $R_{\mathrm{m}}$ is $1 \cdot 5 \mathrm{k} \Omega$, therefore VR1 should not
exceed $15 \mathrm{k} \Omega$. The initial selection of $10 \mathrm{k} \Omega$ for VRI appears to be quite reasonable; the compromise required in this example must be made with the value selected for R1. This may be done as follows.

## SET MID-SCALE INDICATION

If a value of $10 \mathrm{k} \Omega$ is selected for VR1, then the maximum acceptable value for R1 may be determined by assuming a $V_{\mathrm{b}(\mathrm{min})}$ value of 13 V . With $I_{\mathrm{m}}=50 \mu \mathrm{~A}$ (f.s.d.), then $7 \cdot 5 \mu \mathrm{~A}\left(I_{\mathrm{s}}\right)$ will flow in VR1 (determined from $I_{\mathrm{s}}=R_{\mathrm{m}} \times I_{\mathrm{m}} / R_{\mathrm{VR}_{1}}$, making $I_{\mathrm{t}}$ equal to $57.5 \mu \mathrm{~A} . \quad R_{\mathrm{s}}$ is determined by $V_{\mathrm{b}(\min )} / I_{\mathrm{t}}$, which equals $13 \mathrm{~V} / 57 \cdot 5 \mu \mathrm{~A}=226 \mathrm{k} \Omega$ ( $220 \mathrm{k} \Omega$ is a preferred value).

The mid-scale indication of the ohmmeter is thus $220 \mathrm{k} \Omega$, which is not very different from the corresponding indication of $260 \mathrm{k} \Omega$ determined for the A-type circuit when $V_{\mathrm{b}}$ equalled 13 V .

In the B-type circuit, however, $R_{1}$ is fixed at $220 \mathrm{k} \Omega$ irrespective of the variations which occur in $V_{\mathrm{b}}$, since the parallel combination of VR1 and $R_{\mathrm{m}}$ is always small enough to be neglected. This is very different from the A-type circuit in which the mid-scale indication changed from $320 \mathrm{k} \Omega$ to $260 \mathrm{k} \Omega$ (due to adjustment variations in VRI) when $V_{\mathrm{b}}$ changed from 16 V to 13 V .

This is a very important observation since it shows that the B-type circuit is inherently more accurate than that of the A-type. Actually, this statement ignores the relative abilities of the two circuits to compensate for variations in the internal resistance $\left(R_{b}\right)$ of the batteries. However, $R_{\mathrm{b}}$ is relatively small in the lowcurrent circuits considered so far, and may therefore be ignored.

## RANGE SELECTION

Now consider the second feature of the B-type circuit-the ability to select a particular resistance range by suitable choice of VR1.

We have just seen that a $10 \mathrm{k} \Omega$ value for VRI sets the mid-scale resistance indication at $220 \mathrm{k} \Omega$. Assuming a low-resistance range with a mid-scale indication of about $1 \mathrm{k} \Omega$ ( 30 times smaller than that obtainable with the corresponding A-type circuit) when $V_{b(\min )}=$ 1.3 V , then $\mathrm{I}_{\mathrm{t}}=\frac{V_{\mathrm{b}(\mathrm{min})}}{\left(R_{1}+R_{\mathrm{p}}\right)}$ where $R_{\mathrm{p}}=\frac{R_{\mathrm{m}} \times R_{\mathrm{VR}}}{\left(R_{\mathrm{m}}+R_{\mathrm{VR}}\right)}$.

The value $R_{\mathrm{p}}$ is now comparable with $R_{1}$ and cannot be ignored; at least, not just yet. Since the mid-scale indication is $1 \mathrm{k} \Omega$, then ( $R_{1}+R_{\mathrm{p}}$ ) must equal $1 \mathrm{k} \Omega$. Thus, $I_{\mathrm{t}}=\frac{1 \mathrm{k} \Omega}{1.3 \mathrm{~V}}=1.3 \mathrm{~mA}$. When the meter is indicating f.s.d. $\left(I_{\mathrm{m}}=50 \mu \mathrm{~A}\right)$, the current ( $I_{\mathrm{s}}$ ) which flows in VR1 must equal ( $I_{\mathrm{t}}-I_{\mathrm{m}}$ ), i.e. $I_{\mathrm{s}}=1 \cdot 3 \mathrm{~mA}$ $-50 \mu \mathrm{~A}=1,250 \mu \mathrm{~A}$. The value of VRI required to absorb this amount of current is therefore equal to $I_{\mathrm{m}} \times R_{\mathrm{m}} / I_{\mathrm{s}}=60$ ohms.
This is the maximum value that VRI is ever likely to require. Now, since this value is so small compared with $R_{\mathrm{m}}(1,500 \Omega)$, the value of $R_{\mathrm{p}}$ can be assumed to equal 60 ohms. Furthermore, since $R_{p}$ is also very small compared with $R_{1}+R_{\mathrm{p}}$, i.e. $1 \mathrm{k} \Omega$, we may further assume that $R_{1}$ equals $1 \mathrm{k} \Omega$. The value required for VRI when $V_{\mathrm{b}(\max )}=1.6 \mathrm{~V}$ and when $I_{\mathrm{m}}=$ f.s.d. $(50 \mu \mathrm{~A})$ is equal to $I_{\mathrm{m}} \times R_{\mathrm{m}} / I_{\mathrm{s}}=48$ ohms.

This is the minimum value that VR1 is ever likely to require. From these two sets of calculations, VRI is required to vary between 48 and 60 ohms, depending upon the value of $V_{b}$; a 100 ohms variable resistor would therefore be a very satisfactory choice.

When using such a resistor value, the minimum setting of 48 ohms would represent a setting of 48 per cent of maximum, which would yield very smooth adjustment during the zeroing procedure. The circuit for this particular ohmmeter is shown in Fig. 6.

## TWO-RANGE OHMMETER CIRCUIT

The B-type circuit can also be used to provide two resistance ranges and, like the A-type circuit, this may be achieved by using two batteries and a single zeroadjustment control. In order to make a more direct comparison with the A-type circuit (Fig. 3), a B-type two-range circuit will be designed using battery voltages of 15 V and 1.5 V , attempting to achieve the same approximate mid-scale indications.
The mid-scale indication for the oнms $\times 10$ range of the A-type circuit, using $V_{\mathrm{b}}=15 \mathrm{~V}$, was found to be $300 \mathrm{k} \Omega$. The nearest approach to this figure using the corresponding B-type circuit, and a value of $10 \mathrm{k} \Omega$ for VR1, was $220 \mathrm{k} \Omega$.
By replacing $V_{\mathrm{b}}$ of the B-type circuit with a battery of 1.5 V , so as to produce a oHMs $\times 1$ range, then the mid-scale indication will be reduced by a factor of ten, making $R_{1}=22 \mathrm{k} \Omega$. The mid-scale indications are, therefore, not widely different from those of the A-type circuit.

However, as was explained when the A-type circuit was examined, the zeroing adjustment of VR1 on the онмs $\times 1$ range of that circuit was expected to be very coarse, because of the compromise which had to be made concerning the choice of value for VR1. Let us now see what the sensitivity of the zeroing adjustment is like in the B-type ohmmeter.

The sensitivity is all right on the ohms $\times 10$ range because VRI was selected to make it so.

## LOW RESISTANCE SETTING

On the ohms $\times 1$ range, the lowest resistance setting required for VRI occurs when $V_{\text {b(max })}=1.6 \mathrm{~V}$; the total current $\left(I_{t}\right)$ in the circuit during the zeroing procedure is equal to $V_{\mathrm{b}(\max )} / R_{1} \simeq 73 \mu \mathrm{~A}$. In this condition, therefore, the value of VR1 must be adjusted so that it absorbs the $23 \mu \mathrm{~A}$ which is in excess of $I_{\mathrm{m}}$, the f.s.d. current of the meter.

Since $I_{\mathrm{s}}=23 \mu \mathrm{~A}$, and $I_{\mathrm{m}} \doteq 50 \mu \mathrm{~A}$, then the required value of VR1 must equal $I_{\mathrm{m}} \times R_{\mathrm{m}} / I_{\mathrm{s}}=3,260$ ohms. A setting of this value represents 33 per cent of $R_{\mathrm{VR}(\max )}$, which represents a substantial angular rotation of the control shaft- the zeroing adjustment will, therefore, be quite smuuth in this worst-case condition, and will be even better when the battery is relatively new. The circuit diagram of this particular two-range ohmmeter is shown in Fig. 7.

## SHUNT OHMMETER

In the shunt ohmmeter (Fig. 8), the indicating meter M1, is connected directly across the input terminals in parallel with the unknown resistor ( Rx ). The circuit is normally used for measuring very low resistance values (typically 0.01 to $2,000 \mathrm{ohms}$ ), and is therefore ideally suitable for measuring the winding resistances of coils and transformers.

The resistance scale differs greatly from the other types of ohmmeters so far examined in.that it reads from left-to-right instead of from right-to-left, i.e. zero ohms corresponds to zero deflection and infinite resistance corresponds to f.s.d.


## SET ZERO

The zeroing procedure is very similar to that adopted for previously described circuits, except that it is carried out with the input terminals open-circuit (corresponding to infinite resistance) instead of with them shortcircuit .
To zero this type of ohmmeter, the input terminals are left open and VR1 is adjusted until the meter indicates f.s.d. (VR1 and R1 have the same purpose as in previously described circuits, and their values are determined by the same procedures.) Having done this the unknown resistor ( Rx ) is then connected to the input terminals. This causes the meter current ( $I_{\mathrm{m}}$ ) to be bypassed to some extent and a reduced indication results; the degree of the reduction depending upon the value of $\mathbf{R x}$. If a short-circuit is connected to the terminals then all of $I_{\mathrm{m}}$ is bypassed and zero indication results.

## RANGE SELECTION

The range of the ohmmeter may be changed by connecting an internal resistor across the meter. This reduces the effective sensitivity of the meter and hence more total current ( $I_{t}$ ) is required to achieve f.s.d.
On the онмs $\times 1$ range no ranging resistor is added and the mid-scale resistance indication is equal to the meter resistance $R_{\mathrm{m}}$, i.e. 1,500 ohms. Thus, if a resistor ( Rx ) of the same value as $R_{\mathrm{m}}$ is connected to the terminals, then $I_{t}$ will be shared equally between Rx and the meter; $25 \mu \mathrm{~A}$ will flow in each.

In order to produce the oHms $\div 10$ range provided for in Fig. 8, an internal resistor R2 must be connected across the meter so that the parallel combination of R 2 and the meter is equal to $R_{\mathrm{m}} / 10$, or $\frac{R_{2} \times R_{\mathrm{m}}}{R_{2}+R_{\mathrm{m}}}$. Rearranging this expression and substituting known values, we get $R_{2}=R_{\mathrm{m}} / 9=1,500 / 9=166 \cdot 6$ ohms.


Fig. 8. Shunt ohmmeter in which the meter is connected directly across the terminals and the range selector

fig. 9: Constant resistance ohmmeter

The same result may be achieved by using the expression

$$
R_{2}=\frac{R_{\mathrm{m}}}{n-1}
$$

where $n$ is the number of times that the f.s.d. is to be multiplied. When operating on this range, $I_{t}$ is increased by a factor of ten $(500 \mu \mathrm{~A}), 90$ per cent of which flows in $\mathbf{R}_{2}$, and the mid-scale indication equals $R_{\mathrm{m}} / 10$ or 150 ohms.

## CONSTANT RESISTANCE OHMMETER

In the constant resistance type of ohmmeter (Fig. 9), the variable resistor VR1 is connected in such a way that the total resistance of the circuit is maintained near-constant as VR1 is adjusted to compensate for changes in $V_{\mathrm{b}}$. This is accomplished by connecting VR1 across the meter in such a way that it is used as a potentiometer.
Adjusting VR1 in one direction causes more resistance to be added in series with the meter and a lower value of resistance to be connected in parallel with Rx ; the reverse occurs when VR1 is adjusted in the opposite direction. This arrangement maintains an almost constant total circuit resistance, and hence the accuracy of the indication is very little affected by the setting of VR1.

Fig. 9 shows a two-range ohmmeter based upon this type of circuit. Only one battery is used and the midscale indications on the oHMs $\times 1$ and oHMs $\times 10$ ranges are $10 \mathrm{k} \Omega$ and $100 \mathrm{k} \Omega$, respectively. The zeroing procedure is conventional and is carried out with the input terminals short-circuited; the ohmmeter scale reads from right-to-left.

This completes this examination of various ohmmeter circuits; there are a great many other types of circuits but these are, in many cases, simply variants of those just described.

## NEWS BRIEFS

## Silicon Pictures

A NEW TV camera tube incorporating a silicon target is being developed by English Electric Valve Co. Ltd. The target of this tube-The Sidicon-is in the form of a mosaic of isolated silicon diodes and its production follows a sequence of modified micro-circuit practices resulting from improved microlithographic techniques.

Results of developments so far, have shown these tubes, which are interchangeable with 1 inch vidicons, to be mechanically, thermally and electrically very rugged, with high sensitivity throughout the visible and infra-red range. The Sidicon has considerably less lag than conventional vidicons and much higher sensitivity. The nature of the targets allows full high-vacuum processing, so ensuring a long life expectancy.

## Brain Box

A Small sensitive electronic amplifier no larger than a packet of cigarettes is helping surgeons at the London Hospital, Whitechapel, to trace brain activity during operations for Parkinson's disease.
This is achieved by picking up and monitoring very small signals from the brain through an electrode implanted in it. The amplifier enables the surgeon to track with greater accuracy the exact portion of the brain in which he is working while carrying out this extremely delicate operation.

Made by the British company, Fenlow Electronics Ltd., it is the first miniature data amplifier the firm has produced for medical use. Using f.e.t.'s the amplifier is constructed to stringent safety specifications and costs only £40.

## Transportable Tactical Centre

The photograph below shows test pattern symbols on the screen of a lightweight display console being checked with a microscope at Hughes Aircraft Company, America, to verify their sharpness and clarity. The console, along with high-speed computers and other electronic equipment, is being built by Hughes for the U.S. Air Force Electronic Systems Division's 407L programme, an advanced concept of tactical air control.

The equipment will be housed in inflatable, modular operations centres that can be transported anywhere in the world and set up in a matter of hours. Hughes is producing 31 of these tactical centres along with two training systems designed to give the Air Force flexible and mobile response to fast-changing battlefield situations.



## WHAT THE ASTRONAUTS SAW

All crews of the Apollo missions reported seeing flashes and streaks before their eyes even when closed. It is supposed that this is the result of the passage of ionised cosmic ray particles through the head.

It has been suggested that the light comes from the passage of the high energy particles through the jelly-like medium in the eyeball where light has a lower velocity. Another explanation is that it is the impact of the particles on the retinal cells.

The particles also affect the astronauts' space helmets which are made of a polycarbonate plastic. This plastic is of the long-chain polymer class and as a result of radiation the molecules are broken up. It is known in biological systems that ionising radiations damage cells by disturbing the replication of long-chain molecules.

It has been found that the damage to the space helmets can be studied by etching the streaks caused by the particles. Silicone casts can be made of the holes in the plastic and the rate of etching indicates the degree of ionisation that takes place. The shape of the rubber allows the measurement of the ionisation from point to point along the track. Comparison with the effects of known ions enables the particular particle to be identified.

## RADIO TELESCOPE

Germany's new 100 m radio telescope, the largest steerable dish in the world, is nearing completion at Effelsberg some 40 km from Bonn. The site is' a deep valley in an area of minimum interference.

The design of this telescope has made use of the most advanced principles of structural engineering to ensure that in all positions of the dish the effects of loading both static and variable cause the least departure from paraboloid form. It is expected that the surface accuracy will hold to less than 1 mm .

The actual construction of the reflecting surface is interesting, the inner section of 60 m diameter is formed from an aluminium sandwich with a honeycomb inner unit bonded to the outer formed sheets. Trial measurements show that the r.m.s. accuracy of the surface of this construction is of the order of 0.22 mm .

The next 20 m of the surface is covered by formed sheets of aluminium supported by aluminium sections. The standard of accuracy reached in this section of the dish is 0.27 mm . The outer section of this ring of panels is connected to the rest of the surface, made up of 6 mm square stainless steel mesh panels, by perforated aluminium panels to maintain the aerodynamic conditions required. The accuracy of the outer mesh is about 0.55 mm .

The overall efficiency of the telescope is expected to be capable of operation down to a wavelength of 5 cm . The central 60 m section will, it is hoped, enable wavelengths of 8 mm to be used.

Round the outer rim of the dish a collar has been added to reduce the effects of local interference.

## FOCUSING ACCURACY

The focus to diameter ratio is midway between that of the Jodrell Bank and Parkes telescopes. Jodrell Bank Mk1 is 0.25 and Parkes 0.41 with the German dish at 0.3 .

The Gregorian system has been adopted which enables both prime focus and secondary focus work to be carried out. For prime focus operation a tube will project through the centre of the subreflector to house a prime focus receiver. The intention is to use multibeam methods of observation and as many as nine feeds will be available at the secondary focus. Space receivers at wavelengths of $6 \mathrm{~cm}, 11 \mathrm{~cm}$, and 13 cm will be provided at the secondary focus.

With such a sophisticated type of radio telescope it is not surpris-
ing that the receiving installation is very elaborate. Cryogenically cooled amplifiers and low noise front ends are being provided.

The timing system will use a rubidium clock as reference for the universal oscillator in line measurements for Pulsar timing and very long base line observations. Continuum measurements will be made by Radiometers.

## COMPUTER CONTROL AND PROCESSING

Data processing is also very elaborate and the basic data processor and steering computer is an ARGUS 500 by Ferranti. This digital computer will co-ordinate transformations, control the telescope drive and process real time data.

From a control desk an observer can choose the astronomical coordinates he needs and the method of scanning. The computer will then carry out the transformations and instruct the drives of the telescope in the necessary velocities in azimuth and elevation.

Since this occupies only a portion of the computer cycle, time is available for storing of data on magnetic tape, operate a fast line printer and Calcomp plotter and have time available for some on-line data processing.

## SUPPORT FOR THE GENERAL THEORY OF RELATIVITY

Working with Mariners 6 and 7 probes, the team at the Jet Propulsion Laboratory led by Dr J. Anderson have obtained data which, they claim, confirms Einstein's predictions with an accuracy of 2 to 4 per cent.

Previous work by Muhleman and Shapiro using the passive radar technique by bouncing signals off planets close to the sun's limb showed an accuracy of 5 per cent.

The first results with active radar are now available from the 210 ft dish at Goldstone. A narrow beam of radio signals at 250 kW is sent out to impinge on Mariner 6 or 7 , which are now some 250 million miles beyond the sun. The spacecraft collect the signals, amplify them, and transmit them to the dish at Goldstone. The round trip takes about 43 minutes and can be timed within a microsecond.

The most important source of error is the very considerable dispersion of radio waves by the sun and the results depend on the type of model of the sun's atmosphere that is used.

Dr Anderson's resuits conflict with the gravitational theories which show about 7 per cent error.


0WNERS of small boats, both power and sail, often find the need for a boat speed indicator. The speed indicator is useful for a variety of reasons including engine tuning, propeller selection, water skiing, sail trimming, arrival time estimation, and the obeyance of speed limits. The device described here uses a potentiometric transducer in a simple circuifto produce a linear speed reading on a moving coil 哲eter.
 linearly to boat speed. Graph (b) is the actual graph of meter reading against probe angle, taken from 0 to 45 degrees; graph (c) is the result of (a) minus (b). Graph (c) is not quite a straight line-as it should be for complete accuracy-but is within 0.3 of a knot or 5 per cent of the true reading, which ever is the greater, and it is felt that this is sufficiently accurate for most purposes.

The boat speed indicator circuit could, of course, have been made to give a perfect straight line for
(c), but this would make it more complicated and expensive to build. If greater accuracy is required a graph such as (c) can be plotted for the completed unit over the full range of speeds, and this graph used for correcting the speed indicated.

A times 2 range is provided to give greater meter movement at low boat speeds and in this mode the accuracy of the unit will depend mainly on the transducer construction.

## CIRCUIT OPERATION

The input voltage is stabilised by RI and Zener diode D1 so that variations in battery voltage will not affect the circuit function unduly.

The resulting 10 V is applied across VR1 and VR2 and the varying voltage at VRI wiper is taken via
range switch S 3 to a voltmeter circuit. The volmeter circuit consists of the appropriate range resistorsR3 and VR3 or R4 and VR4-diode D2 and the $500 \mu \mathrm{~A}$ f.s.d. moving coil meter M1. The diode is used as a low voltage Zener; its breakdown voltage in the forward bias condition is 0.6 V . This means that up to 0.6 V can be present across D 2 without the meter indicating any current. Once the breakdown voltage is exceeded the diode resistance drops to a low value and the circuit acts essentially as a normal voltmeter.

Potentiometer VR2 is preset to give a reading of 0.01 milliamps on M1 with the wiper of VR1 turned towards VR2 end; this indicates that D2 is just beginning to conduct and as soon as VR1 is varied M1 will indicate the voltage present at its wiper.

Fig. I. Circuit diagram of the boat speed indicator. Reference is made in the text to the supply voltoge, RI and LPI. The tinted panel indicates the potentiometer used in the transducer.

## COMPONENTS . .

## Resistors

RI $220 \Omega$ or $2 \cdot 2 \mathrm{k} \Omega$ (see text)
R2 $20 \mathrm{k} \Omega$
R3 lk $\Omega$
R4 lk $\Omega$
All $\downarrow$ W, $\pm 10 \%$ carbon
Potentiometers
VRI $5 k \Omega$ high quality sealed carbon lin (see text)
VR2 $2 k \Omega$
VR3 $5 k \Omega$ wirewound trimmers
VR4 Ik $\Omega$
Diodes
DI ZLIO 1.5W, IOV Zener
D2 IN4I48 silicon

## Switches

SI D.P.D.T. toggle
S2 S.P.S.T. pushbutton
S3 S.P.D.T. toggle
Miscellaneous
MI $500 \mu \mathrm{~A}$ f.s.d. moving coil meter (S.E.W. edgewise type)
SKI/PLI Two pin DIN plug and socket
SK2/PL2 Three pin DIN plug and socket
LPI Miniature indicator lamp and holder (voltage to suit supply)
Veroboard 2 年in $\times 3$ itin $\times 0.1$ in matrix
Diecast case $6 \frac{3}{\text { a }} \mathrm{in} \times 4 \frac{3}{2} \mathrm{in} \times 2$ tin
Connecting wire, transducer connection wire3 core plastics covered mains lead; supply connection wire-2 core plastics covered mains lead.
6B.A. fixings
Foam rubber, paint and Letraset


The action of D2 provides the required circuit response to variation of VR1.

Switch S2 and resistor R2 provide a circuit voltage checking position that will indicate, by way of MI, when the battery voltage is too low to operate the circuit. Resistor RI will be either 220 ohms or 2.2 kilohms to accommodate supplies of 11 V to 18 V or 18 V to 50 V d.c. respectively; LP1 will, of course, have to be the correct voltage for the supply.


Fig. 2. Groph of probe rotation against meter reading (b) subtracted from the $\operatorname{Cos}^{2} \theta$ graph (a) to give the resultant curve (c). For an accurate instrument curve (c) should be a stralght line


## TRANSDUCER CONSTRUCTION

The transducer must be constructed of materials that will not be affected by water; in the prototype brass was used throughout. The shaft is a model boat propeller shaft and the gears are nylon, 2 to 1 ratio, also supplied for model making. The torsion spring can be any $\frac{1}{2}$ in diameter coil spring that is of fairly light construction. Particular attention should be paid to accuracy since any unnecessary friction or play in the unit will result in inaccurate and erratic readings when in use.

The gears should be arranged to mesh closely and there should be as little play in the potentiometer bearings as possible; because of this a metal encased potentiometer may prove best in this application-this can be sealed with epoxy resin or paint if necessary. Before using the transducer all surfaces should be protected with paint or varnish, the shaft and potentiometer bearing packed with grease and the container sealed with a rubber ring.

Details of the transducer are given in Fig. 3. Three $\frac{1}{8}$ in diameter brass rods are used to position the two plates; one of these rods forms a locating pin to ensure correct orientation of the probe with respect to boat axis.

The other two pins form rotation limiters for the arm connected to VRI and a spring anchoring point. The locating pin slides into a hole in the mounting bracket (shown in Fig. 3), that is fixed to the transom of the boat. The complete transducer can be lifted clear of the water, for breaching purposes or mooring, without completely removing the unit.

## TRANSDUCER ASSEMBLY

Assembly of the transducer may prove slightly tricky, but is fairly easy once the correct sequency is known. When all parts have been made to the details shown in Fig. 3 the three rods can be soldered or brazed to the lower plate-the one with no potentiometer mounting hole. The locating pin should be affixed so that its top end is about $\frac{1}{16}$ in above the position of the upper plate-determined by the depth of VR1. The remaining two pins are mounted so that their lower end is flush with the underside of the lower plate.

Next, VRI should be mounted on the upper plate approximately in the centre of the slightly elongated hole. It is not necessary to tighten the fixing fully at this stage since the horizontal position of VR1 will have to be adjusted. Fit the spacers over the pins and place the two plates together, holding them with the two screws and two further spacers; the case lid should not be included under the screw heads at this stage.

The next operation is to mount the small gear on the potentiometer using the spindle coupler. The shaft can then be inserted through the two plates and the larger gear attached by tapping the brass bush 4B.A. and screwing it to the spindle.

## SHAFT ALIGNMENT

The vertical position of the shaft can now be adjusted so that the two gears align-a small washer should be inserted under the large gear-the shaft is then soldered or brazed to the lower plate. The two screws can be removed and the case lid slid over the shaft and locating pin and the whole thing screwed together. The rotation limit arm is inserted so that with the arm touching the anti-clockwise limit pin, VRI is turned so that it is a few degrees off its fully anti-clockwise position. VRI can now be adjusted so that the two gears mesh correctly and its fixing tightened fully.

The torsion spring can now be fixed, the spindle revolved so that slight torsion is applied and, with the mounting bracket in place, the probe bolted in position. A washer should be included between the shaft and the probe and the probe fixed so that there is no vertical play on the spindle. The probe is made by hammering flat one end of a $\frac{3}{16} \mathrm{in}$ diameter brass rod, shaping and drilling the flattened end.

## INDICATOR CONSTRUCTION

The four resistors, the two diodes, D1, D2 and VR2, VR3 and VR4, are mounted on a small piece of Veroboard, as shown in Fig. 4. Veroboard is used as it provides good support to the components and is not badly affected by water, as some tag panels are.


Fig. 3a. Exploded view of the complete transducer, the torsien spring is shaped from a long tension spring and is affixed to one of


## TRANSDUCER MATERIALS. . .

16 s.w.g. brass plate, 2 in $\times 10 \mathrm{in}-$ for plates and bracket; $\frac{1}{8}$ in diameter brass rod, 8 in -for pins; $\frac{3}{16}$ in diameter brass rod, 6 in-for probe
Model boat propeller shaft and spindle-see text
Model makers' nylon gears $2: 1$ reduction with $\frac{1}{4}$ in diameter brass bushes
Spindle coupler $\frac{3}{4}$ in long, for $\frac{1}{4}$ in diameter spindles Spacers $\frac{1}{4}$ in $\times \frac{1}{\frac{1}{8}}$ in internal diameter, brass ( 40 ff )
6B.A. screws $1 \frac{1}{2}$ in long ( 3 off) for fixing screws and rotation limit arm
Case, 3 in internal diameter plastics container with flat screw top
Spring $\frac{1}{2}$ in diameter tension spring of light construction at least $1 \frac{1}{2}$ in long.
Grommets ( 3 off) - 2 to suit shaft and Ifor connection lead; 4BA and 6BA nuts and washers

Fig. 3b. Drilling details of the transducer plates. The distance between the two plates is determined by the depth of the potentiometer body-thus rod and spacer length wIII vary. Two plates are required and these should be drilled while clamped together. The elongated hole is only drilled through one plate. The position of the plates when mounted inside the case is indicated


Fig. 3c. Transducer mounting bracket details. Holes marked "D" must line up when the bracket is bent, their sire will depend on the shaft and grommet diameter

Fig. 4. Veroboard layout and wiring diagram. The potentiometers may be designated as shown on the board, for easy identification during setting up and calibration

Fig. 5. Layout and wiring diagram of all components mounted in the die-cast case. The lid to the case forms the base of the unit and the view shown is of the underside with the base plate removed


The remainder of the components are mounted directly to the die-cast case used to house the unit, see Fig. 5. This case should be carefully painted inside and out, after drilling, to prevent it being corroded by salt water; the base plate should be sealed with rubber strips. Sockets are provided for the leads to the transducer and the supply; these leads should be of good quality plastics insulated flex.

The meter is mounted on a rubber pad to provide some shock protection and prevent water from entering the case. The meter specified has no external apertures and the mechanical zero is adjusted through a hole in the top of the case which is plugged with a small piece of rubber when not in use. The Veroboard is mounted by sandwiching it between two pieces of foam rubber.

Layout and wiring of all components mounted in the indicator case is shown in Fig. 6. Internal batteries may be used if a larger housing is provided; in this case LP1 should be omitted to conserve the battery.

## INSTALLATION

The mounting bracket is fitted to the transom of the boat so that the lowest part of the bracket is about lin above the highest possible water line. The bracket should be fitted well away from propellers on power craft or any obstruction that could interfere with the water flow.

The length of the shaft used will depend on the type and speed of the boat. The prototype, which was intended for a sailing dinghy, used a 9 in shaft,
but power yachts may require a greater length to keep the probe below and the unit above, the water level at all speeds (the transducer body should also be clear of the water when going astern).

The indicator unit can be fitted in a convenient position and a good quality piece of 3 core mains lead made the correct length and wired to PL2. The transducer could be fitted through the bottom of larger craft but a special adaptor will have to be manufactured for this.

## CALIBRATION

The first step in calibration of the unit is to mark the correct supply level on MI. To do this a d.c. voltmeter is used to measure the voltage across D1; this voltage should be 10 V -providing the battery is in good condition and D1 is functioning. Once this has been checked S 2 can be depressed and the reading of M1 noted and marked on the scale or meter face; VR1 should be in circuit at its stationary position for this operation.


Switch S3 can then be set to the first range ( $\times$ 1) and VR2 adjusted so that the meter shows a reading of 10 MA . Once this is done the meter can be zeroed when the circuit is energised, using the mechanical zero adjustment.

The maximum possible speed of the boat should be estimated and this speed marked at the full scale deflection point on M1. The scale should then be 'divided equally to indicate the intermediate speeds. With the probe rotated through 45 degrees, VR3 should be set to indicate full scale deflection on M I

## INITIAL SETTING

Initial setting of VR3 can be made without installing the unit. Once this is completed the unit should be installed for further calibration in the boat in which it is to be used, in the correct position with the transducer lead of the required length.

Initial calibration is by means of variation of probe length and diameter (prototype used a 4 in shaft of $\frac{3}{16}$ in diameter brass) and torsion spring. Probe diameter may easily be increased by sliding a length of plastics flex insulation over it. Fine calibration may be effected by adjustment of VR3. The unit should be calibrated as near the maximum speed as possible, since this is the point at which the circuit is most accurate (refer to Fig. 2).


There are two ways of speed calibrating the unit: by comparison with another speed indicator or by timing the boat over a measured distance. If the second method is used the measured distance should be as large as practicable and the boat speed held constant by means of the indicator, any error can then be adjusted after a second run in the opposite direction.

To calibrate the times 2 range it is only necessary to hold the probe in such a position that half full scale deflection is indicated with S3 in the $\times 1$ position; then switch S3 to $\times 2$ (with the probe in the same position) and adjust VR4 to give full scate deflection on M1. When this has been done the probe fixing can be soldered over, to protect it and prevent it becoming corroded, and finally painted

Designations may then be added to the unit as required, using Letraset, and given a coat of clear varnish to protect them. The unit is then ready for use.

If it is found that the meter is too sensitive to slight variations in speed or that the needle tends to flicker in use, the movement can be damped by placing a $2,000 \mu \mathrm{~F} \quad 15 \mathrm{~V}$ electrolytic capacitor directly across the meter terminals-observing polarity. $\star$


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## DIGITAL DICE

Perhaps your readers would be interested in the following circuit for an Electronic Dice.
The circuit is basically three binary stages with feed-back to give a count of six, being driven at high frequency by a free running multivibrator. When the count is stopped by pressing the display button S1 the output of the six counter is fed via gates to light lamps LP1 to LP6, giving a display in the familiar dice combinations, i.e. with the centre lamp only lit for a "one", the six outer lamps for a "six", etc. The dice requires only four decoding circuits;

the first of these decides "even or odd"-if the count is odd only the centre lamp lights. The next gate decides "not one" which lights two diagonally opposite lamps (except during a one). A third gating circuit decides four, five or six and lights the two remaining diagonally opposite bulbs on these counts. The final gate decides "six" and lights the two remaining bulbs on this count. A little thought will show that these combinations will automatically light the proper number of bulbs in the correct pattern for each dice position. The block schematic diagram of the dice is shown in Fig. 1; Figs. 2, 3, 4 and 5 show the sections of circuitry, Fig. 2 being the driving multivibrator; Fig. 3 is the divide by 6 counter; Fig. 4 shows the five gates that together form the three gateing circuits and Fig. 5 shows the lamp driver cịrcuits.

The display panel is made up of a square of holes drilled in the positions shown in Fig. 6. A piece of coloured translucent perspex is fitted over a blanking panel, so that only the illuminated lamps can be seen as spots of light on the perspex.

If required, the dice may be built up as a double unit in which case the divider board, gates and lamp display should be duplicated and the second divider board input driven from point "D" on the first divider board; this ensures independent displays on the two dice.

The circuit may be powered either by a nine volt dry battery or by a d.c. nine volt, one amp, mains power supply. The mains power supply is preferable due to the current drain of the lamp display.
J. D. Croft,

Warrington, Lancashire.

| Count | Output from $\div$ counter |  |  |  | Binary |
| :---: | :---: | :---: | :---: | :---: | :---: |
|  | A | 8 | C | D |  |
| 1 | NEG | POS | POS | POS | 000 |
| 2 | POS | NEG | POS | POS | 001 |
| 3 | MEG | POS | NEG | POS | 010 |
| 4 | POS | NEG | NEG | POS | 011 |
| 5 | NEG | POS | NEG | NEG | 110 |
| 6 | POS | NEG | NEG | NEG | 111 |



Fig. 2. Multivibrator driver for the dice

Fig. 3. The divide by six counter

Fig. 4. Gate circuits used in the dice

Fig. 5. Lamp driver circuits; all lamps 6.3 V 0.04 A


II is often required to obtain a staircase waveform output from 1, 2, 4, 8 counter or logic outputs. The methods usually used are combinations of integrators and diode pumps of various descriptions. The circuit used here, however, is purely digital and the minimum of design application and components are required. The components used may be four transistors, used as single input gates, four Zener diodes and a load resistor. All of the components could probably be incorporated economically on a single i.c.

For operation of this circuit, I will refer to the circuit diagram (Fig. 1) where the resistors R1, R2, R3, and R4 ensure that the transistors TR1, TR2, TR3 and TR4 are saturated when the inputs $1,2,4$, and 8 are at logic " 1 ". (which must be 10 V or more in this circuit).

In " 0 " output condition the transistors TR1, TR2 and TR3 and TR4 will all be saturated and the output will be at a level of $V_{\text {ce(sat }} \times 4$ above zero volts or ground, this gives a level of approximately $1 \cdot 2 \mathrm{~V}$. Now assume input 1 is taken to zero volts. or ground, TR1 will thus switch off; the voltage across which will rise until D1 Zener diode break-down level is reached. This break-down voltage level is selected to be 1 volt plus the $V_{\text {ce(sat) }}$ of TR1, this will give a step of 1 volt at the output. The voltage $1 \times V_{\text {ce(sat) }}$ is added to each Zener voltage to maintain linear 1 volt steps at the output, as without taking this into account the voltage output will vary depending on the number of transistors saturated or not.

Assume the inputs to be obtained from a binary counter then input 2 will become zero and input 1 will
go to a positive voltage. Thus TRI will saturate shorting out Zener diode D1, but TR2 is now switched off-the voltage across which rises to the Zener break-down voltage of D2. This has been selected as 2 volts plus $V_{\text {ce(sal) }}$ of TR2 which gives an output level of 2 volts above the zero level of $V_{\text {ce }(\text { sat })} \times 4$.

This is continued for inputs 1 and 2 where both TR1 and TR2 are switched off which allows the output to rise by 3 volts i.e., D1 plus D2, and like-wise all the way along the chain of a $1,2,4,8$ counter or other input.
The output will start at $V_{\text {ce }(\text { sat })} \times 4$ (which is zero) and ascend in one volt steps until the output voltage reaches ten volts, our count of ten plus $V_{\text {ce(8si })} \times 4$, this gives a total of 11.2 volts, and it goes without saying the steps may, ascend in level by reversing the logic input levels.

The beauty of this circuit is that it is entirely independent of frequency and voltage levels, providing $V_{\mathrm{CC}}$ does not fall to below the sum of the total Zener voltage levels, i.e. $V_{\mathrm{CC}}$ may be 100 volts (if the components will take it) and the output levels obtained will not vary considerably from those when $V_{\mathrm{CC}}$ was at 12 volts. So it can be seen that the only design consideration is one of upper operating frequency which is dependent upon the components used and not so much the circuit; by selecting the appropriate Zener voltage levels this circuit may be used on various coded outputs quite easily.
D. W. Lloyd, Stotfold, Herts.


Fig. I.


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00 50p
$\begin{array}{rr}50 & 50 p \\ 100 & 50 p\end{array}$
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## LOUDSPEAKERS AND ENCLOSURES

An increasing number of cost conscious hi fi enthusiasts are home constructing loudspeaker systems from the expanding range of multiunit kits and individual loudspeakers now available.

One of these multi-unit kits is the Peerless $20-3$ from P. F. \& A. R. Helme. This is a 3 -way system consisting a low frequency "woofer" loudspeaker with rubber roll surround, a mid-range speaker, a "tweeter" high frequency speaker and a printed circuit board crossover unit.

Recommended for amplifiers of 10 to 40 watts, the maximum power input of the system is 40 watts. The frequency range is claimed to be 40 to $20,000 \mathrm{~Hz}$ and the crossover frequencies are 1,500 and $6,000 \mathrm{~Hz}$. All speakers have voice coils wound on an aluminium coil former and have standard impedances of 4,8 or 16 ohms.

The Peerless 20-3 kit costs approximately $£ 18.87$ and full details will be supplied by A. F. \& A. R. Helme, Summerbridge, Harrogate, Yorkshire, HG3 4DR.

For those readers who do not feel sufficiently proficient to make their own enclosures, Messrs. Omar Skinner \& Sons produce ready built enclosures to makers' specifications for the more popular systems.

The enclosures are soundly constructed and available in a variety of finishes. The baffle boards are cut to order and they claim they can supply an enclosure for every need.

Our photograph shows the Omar Skinner enclosure for the four loudspeaker EMI 750 kit . The 750 kit consists of a bass, mid-range and two treble speakers, which together are capable of handling 20 watts and cover the frequency range of approximately 30 $20,000 \mathrm{~Hz}$. A crossover unit with a choice of switching frequencies. wiring harness and full instructions is included and the complete EMI 750 kit costs $£ 27.50$.

Details of enclosures may be obtained from Messrs. Omar Skinner \& Sons, Warfield Park

Workshops, Warfield Park, Bracknell. Berkshire, and enquiries for information on EMI loudspeaker kits and enclosures should be addressed to EMI Sound Products Ltd., Blythe Road, Hayes, Middx.

## TOOL KITS

During the last few years manufacturers have been gradually gearing themselves to continental specifications and component practices when designing equipment. The result of this gradual changeover has meant that numerous pieces of equipment have contained both U.K. and continental components, i.e. Phillips, Allen, and standard screws.

One of the problems encountered by this situation is the lack of necessary tools when carrying out service repair work. Special Products Distributors seem to have recognised this problem and are now introducing the well-known Xcelite tools from America to the British market.

The first tools to be marketed are a 19 -piece screwdriver kit, 14-piece socket set and a 5 -piece screwdriver kit.

The XL-70 19-piece kit contains a selection of Allen keys, slotted and Phillips screwdrivers, reversible ratchet and extension handle. The ratchet can be attached to the extension handle for added torque if required. This kit is particularly useful for television service engineers.

The 1001 14-piece socket set includes sockets from $\frac{3}{1} \frac{3}{5} \mathrm{in}$. to $\frac{1}{2} \mathrm{in}$., 2 in . extension, reversible ratchet and extension handle.

Included amongst the sockets are two 10 -point sockets, $\frac{1}{4}$. and $\frac{1}{10}$ in., which are dual purpose to fit both square and hexagonal nuts. The reversible ratchet in this kit is fully enclosed to keep out dirt and grit.

The XL. 755 -piece kit is contained in a plastics wallet and is a small set of slotted and Phillips screwdrivers with an offset ratchet handle, again extremely useful for working in awkward and confined spaces.
The XL70 screwdriver kit costs $£ 6 \cdot 25$, the 1001 socket set costs $£ 7 \cdot 18$ and the XL 75 costs $£ 2 \cdot 10$.

Both the XL70 and the 1001 kits are housed in moulded high impact plastics cases. Full particulars of these tools are available from Special Products Distributors Ltd., 81 Piccadilly, London, WIV 0HL.


Peerless 20-3 kit from P. F. \& A. R. Helme

EMI 750 kit housed in an Omar Skinner enclosure



THis article describes the construction of a completely electronic door bell which is simple, cheap, and does not require accurate adjustment. The rhythm and melody are continually changing so that each time the bell push is depressed a different sound is produced.

## CIRCUIT BLOCKS

In the block diagram of the unit shown in Fig. 1, the 250 Hz multivibrator produces the basic note. The base resistors controlling the frequency are divided into two so that the two low frequency ( 1 Hz ) multivibrator circuits can short circuit the upper resistors. A total of four notes is thus obtained using only three switching circuits.

Since the multivibrator circuits run asynchronously the rhythm will be continually changing which means that a different tune will be obtained each time the bell push Sl is depressed.
The output from the 250 Hz multivibrator is fed via an AND gate to amplifier A2 to drive the loudspeaker LS1. The signal is allowed through the gate when the monostable is pulsed, the duration of which may be adjusted between 0.5 and 12 seconds.

A buffer amplifier, A1, precedes the monostable stage and provides the triggering action when the bell push is used.

## DETAILED OPERATION

Transistors TR3 and TR4 in Fig. 2 form the main astable circuit which provides low frequency calculated by $1 / 0 \cdot 7\left[C_{3}\left(R_{5}+R_{7}\right)+C_{4}\left(R_{8}+R_{9}\right)\right] \mathrm{Hz}$.

In order that diodes D1 and D2 effectively short circuit R6 and R8, R7 must be greater than R6 and R9 must be greater than R8.


TR5 and TR6 form another astable circuit working at a very low frequency of about 1 Hz . With R12=R13 and $\mathrm{C} 5=\mathrm{C} 6$ the frequency is given by $1 / 1 \cdot 4 C_{5} R_{12} \mathrm{~Hz}$.

When TR 5 is hard on, the collector is almost zero volts and diode D2 is back biased since the junction of R8 and R9 is always positive. When TR5 is cut off the collector is +6 V and D 2 is forward biased which effectively short circuits R8 and consequently changes the operating frequency of the 250 Hz astable.

The action of TR1/TR2 astable circuit is identical to this but is applied to D1.

## GATING THE OUTPUT

The output is taken from TR3 collector and gated at the input of the amplifier A2 by diode D3. With the bell switch not made TR11 in the monostable circuit will be normally hard on and thus the collector will be nearly at zero volts. Here the diode D4 is forward biased and the junction of R28 and R29 will be held at zero volts irrespective of the input to D3.

TR9 is held on by the positive voltage appearing at the junction of R19 and the lamp. When the bell push is depressed the base of TR9 is brought to nearly zero volts so that it switches off.

With TR9 cut off, the collector will change from zero volts to +6 V . This positive going voltage turns TR10 on via C10 and R23 thus triggering the monostable action of TR10 and TR11. TR11 is turned off and the collector changes to +6 V which reverse biases diode D4, so allowing D3 to pass the output of TR3 to the amplifier A2.

Irrespective of whether the bell push is maintained depressed or not the monostable action will end after a time given by $0.7 \times \mathrm{C} 11 \times($ VR1 $+\mathrm{R} 25)$. In this period a short burst of notes will be obtained. With VRI set to zero the duration will be approximately 0.5 seconds. Set to maximum resistance it will be about 12 seconds.

R21 is included to reduce the voltage to the astable and monostable circuits so that 6 V working capacitors can be used. C9 decouples the astable circuits.

## POWER SUPPLY

The circuit diagram of the power supply is shown in Fig. 3. Here the total current required will depend, in the main, on the rating of LP1.

If a Friedland bell push is used the lamp voltage will probably be $8-15$ volts. Thus a 12 volt transformer would be suitable.

The prototype was powered from a 12-0-12 volt transformer and using a Friedland Type ' $A$ ' lamp the following measurements were made.

| Normal current <br> Bell operating | 150 mA |
| :--- | :--- |
| Bell push held <br> depressed | 1.2 amps |

## Components

| Resistors |  |  |  |  |  |
| :---: | :---: | :---: | :---: | :---: | :---: |
| RI | $1 \mathrm{k} \Omega$ | RII | $1 \mathrm{k} \Omega$ | R21 | $220 \Omega \cdot \mathrm{~W}$ |
| R2 | $22 \mathrm{k} \Omega$ | R12 | $22 \mathrm{k} \Omega$ | R22 | $1 \mathrm{k} \Omega^{\text {. }}$. |
| R3 | $22 \mathrm{k} \Omega$ | R13 | 22k $\Omega$ | R23 | $100 \mathrm{k} \Omega$ |
| R4 | $1 \mathrm{k} \Omega$ | R14 | $1 \mathrm{k} \Omega$ | R24 | $1.8 \mathrm{k} \Omega$ |
| R5 | $3.3 \mathrm{k} \Omega$ | R15 | $6.8 \mathrm{k} \Omega$ | R25 | $2 \cdot 2 \mathrm{k} \Omega$ |
| R6 | $22 \mathrm{k} \Omega$ | R16 | $150 \Omega$ | R26 | $22 \mathrm{k} \Omega$ |
| R7 | $33 \mathrm{k} \Omega$ | RI7 | 10』 2 W | R27 | $1.8 \mathrm{k} \Omega$ |
| R8 | $27 \mathrm{k} \Omega$ | R18 | $15 \Omega 2 \mathrm{~W}$ | R28 | $1 \mathrm{k} \Omega$ |
| R9 | $33 \mathrm{k} \Omega$ | R19 | $15 \Omega 10 \mathrm{~W}$ | R29 | $1 \mathrm{k} \Omega$ |
| R10 | $3 \cdot 3 \mathrm{k} \Omega$ | R20 | $5.6 \mathrm{k} \Omega$ |  |  |

Potentiometers
VRI $47 \mathrm{k} \Omega$ Vertical preset VR2 25 $\Omega$ Preset

Transformer
TI I2V 2A centre tapped (Douglas MT7I)

| Cl | $32 \mu \mathrm{~F}$ elect. 6 V |
| :--- | :--- |
| C 2 | $32 \mu \mathrm{~F}$ elect. 6 V |
| C 3 | $0.01 \mu \mathrm{~F}$ |
| C 4 | $0.01 \mu \mathrm{~F}$ |
| C 5 | $32 \mu \mathrm{~F}$ elect. 6 V |
| C 6 | $32 \mu \mathrm{~F}$ elect. 6 V |

C7
$250 \mu \mathrm{~F}$ elect. 15 V
C9 $250 \mu \mathrm{~F}$ elect. 6 V
$10 \quad 0.1 \mu \mathrm{~F}$
CII $250_{\mu} \mathrm{F} 6 \mathrm{~V}$
Cl2 $5,000 \mu \mathrm{~F}$ elect. 15 V

Transistors
TRI-TR7 BCIO8 (7 off)
TR8, OC28
TR9-TRII BCIO8 (3 off)
Diodes
DI-D4 OA90 (4 off)
D5-D8 RS50AF (4 off)

## Miscellaneous

SI (see text), LSI 3-15 ohms loudspeaker,
Veroboard $0 \cdot 1$ in matrix $4 \frac{1}{2} i n \times 6 i n$ and $2 \frac{1}{2} i n \times 5 i n$.


Fig. 2. Circuit diagram of Doorbell Yodeller


Fig. 4. Component assembly of (a) the astable and amplifier circuit; (b) the monostable and switching amplifier. Assembly may be combined on a single Veroboard

(b)


## CONSTRUCTION

In the prototype the astable and amplifier circuits were built on a piece of 6 in by $4 \frac{1}{2}$ in Veroboard as given in Fig. 4. Here there is ample room for the components and no breaks in the copper strip are required.
A $2 \frac{1}{2}$ in by 5 in Veroboard is used for assembling the monostable circuit and switching transistor TR9. The reason for this separate board construction is because the monostable is dispensable since it only provides an interval of tones, the period of which can be set by VR1.

Since there is nothing critical in the layout, single board construction for the complete circuit, including power supply, can be made.

## CHECK OUT

If the completed unit fails to function with the supply applied, the following check out procedure should be undertaken.

First disconnect D4 to isolate the monostable. If a tone is not apparent, connect a headset via crocodile clips between TR3 collector and emitter. No sound points to either TR 3 or TR4 being defunct.
If the stage is alright, apply the 'phones to TR7 and TR8 collectors, in that order, to determine the offending transistor.

To check the operation of the low frequency astables, a voltmeter should be connected to the collectors. This method can be used to establish the switching action at TR9 collector, the swing here being between 0 and 6 V when the bell push is depressed.

Once the circuit is functioning correctly R6 can be replaced by a preset potentiometer if any time adjustment is required.

## VARIATIONS

As already mentioned the monostable section could be omitted. Simply omit TR10, TR11 and their associated components. Also omit C10 and R23 and connect the collector of TR9 directly to D4.

If an illuminated bell push is not used connect a 100 ohm resistor across the bell push contacts. This can be done on the component board.

If the monostable action is not required and a nonilluminated bell push is used, connect TR 3 collector directly to R15, the base resistor of TR7. The bell push may then be used to connect the dc supply to the circuit. A 6 volt transformer could be used in this case.

A wooden box, or metal case, can be used for housing the completed circuitry, here the only external control item will be the potentiometer VR2.

## NEWS BRIEFS

## Trinitron T.V.

ANEW colour television tube-called the Trinitron has been announced by Sony Ltd. The tube uses only one electron gun that projects three electron beams; the beams are converged and focused through two large diameter electron "lenses" and a pair of deflectors. Because a large diameter single "lens" can be used to focus all three beams from the Trinitron gun, greater brightness and better focus are claimed to be achieved.

The tube shown below next to a conventional tube) also utilises a new colour selection method named "Apeture Grill" which uses a vertical slotted grill and vertical lines of phosphers rather than the holes and dots of the normal shadowmask tube. The single gun can also be used with either a shadowmask tube, or a chromatron tube, as can be seen from the drawing below.

The new tube has been incorporated in a 13 in screen colour television which, when recently demonstrated to the press, gave a good account of itself. The set will be on the market in this country in April ' 71 and will retail at just under $£ 200$. It will be interesting to see if Telefunken A.E.G. are prepared to allow Sony to market this set, if it infringes their patent on the P.A.L. colour system, without a legal fight. It is not yet possible to say if the set infringes P.A.L: patent since Sony will give no technical circuit data, it will also be interesting to see if Sony can mak larger screen sets-even if, as they state, they do not wish to market them in this country.



PART TEN-By R. W. COLES
METAL OXIDE SILICON LOGIC (MOS)
$T$ was mentioned in an earlier article in this series, that a further two logic families have been elevated to positions which rank them alongside the three originally basic groups RTL, DTL, and TTL.

This article concerns itself with the first of these two comparative newcomers, Metal Oxide Silicon Logic, usually referred to simply as MOS.

## MOS DEVICE CAPABILITY

MOS logic is a very different family from any of the others discussed, both in fabrication and application. Instead of conventional bipolar transistors, insulated gate field effect devices are employed, and in general no linear resistors or diodes are used at all.

MOS is used with negative supply voltages of up to 30 V , with consequently large logic swings which render the mixing of this family with, say, TTL a complicated business usually requiring special "interface" circuitry.

Registers and gates in the MOS range will not run at the high speeds associated with TTL either, a limit of 1 MHz being common in the specification of a shift register package.

In the light of all these apparent disadvantages one may well ask why anyone should bother with these devices at all, and the answer to this is that MOS is very simple indeed to produce, an advantage which makes it possible to incorporate vast quantities of logic elements on a single chip, and still achieve an economic yield.

A bipolar device, whether it be a single transistor or an MSI counter, requires well over one hundred process steps in its manufacture from a silicon "chip". An MOS circuit on the other hand is produced in less than forty steps of comparable complexity, which means less chance of manufacturing discrepancies and a correspondingly lower reject rate on circuits of the same magnitude as their bipolar counterparts.

Usually this improvement is used to advantage to enable large logic arrays, such as dual 100 -bit serial shift registers, to be built on one chip, rather than duplicate the bipolar circuits. This slant towards large scale integration (LSI) is also helped by the fact that an MOS transistor, being a low current, high impedance device, takes up only about one fiftieth of the chip area that a typical bipolar device needs.

MOS techniques are beginning to revolutionise many areas of logic design because of this capability of producing complete systems in one package. As an example, a recently introduced three digit multimeter uses a single LSI MOS chip which contains all the analogue-to-digital conversation logic and display decoding required, all in a 16 -pin dual in-line package.

## STRUCTURE

Transistors of the MOS type have been around for some time now, and have appeared in many designs, in particular the "front ends" of communications receivers, and high impedance input stages for audio amplifiers. Readers will be more familiar with them as field effect transistors (f.e.t.).

Just as there are $p n p$ and $n p n$ bipolar devices, so there are $p$-channel and $n$-channel f.e.t.s, but in this case there is a further division into "enhancement" and "depletion" modes of operation, giving four device types in all. MOS logic circuits generally employ p-channel enhancement mode devices, although there is a recent form which uses complementary ( $p$ - and $n$-channel) logic on the same chip. The difference between $p$ - and $n$-channel devices will be obvious to most readers, but "enhancement" and "depletion" may call for some explanation.

Fig. 10 shows the operation of these two devices in diagrammatic form. F.e.t.s have three electrodes known as the source, the drain, and the gate, and in the MOSFET the aluminium deposition known

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\& 80 p \& $32+32 / 450 \mathrm{~V}, ~$ \& 88 p
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| 20F2 | 0.87 | DK91 | 0.28 | El33 | 0.48 | PCF802 | 0.45 | U329 | 0.78 | $0 \mathrm{C81} 1 \mathrm{D}$ | 0.12 |
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Fig. 10.1a. P-channel enhancement mode device
FIg. 10.1b. P-channel depletion mode device


Fig. 10.2. Construction of the f.e.t. in MOS logle (left) with theoretically correct and simplified versions of the circuit symbol


Fig. 10.3a. Logic Inverter with discrete resistor as a load

Fig. 10.36. Using an MOS transistor In place of the resistive load
as the gate is insulated from the other sections of the device by a layer of silicon dioxide. There is therefore no d.c. current flow into or out of the gate, and the input impedance is extremely high, only the field set up by the gate voltage is used to modulate the current flow from source to drain.

When the gate voltage is such that there is a current flow between the other two terminals, a "channel" is said to exist between them. It is the type of bias necessary to form this channel which sets the difference between the enhancement and depletion devices.

## ENHANCEMENT MODE

In the enhancement mode a channel does not exist between source and drain until an appropriate gate bias is applied, whereas in the depletion mode a channel exists with zero gate bias, and a bias has to be applied to cut off current flow. In Fig. 10.1a, for example, the $p$-channel enhancement mode device requires a negative bias on the gate before it will form a channel, but in Fig. 10.1b the $p$-channel depletion mode device will have a channel unless the gate is biased positively.

Of these two types the enhancement device is more suited for use as a logic switch, because it is off until turned on by a negative bias from a previous stage.

Fig. 10.2 compares the construction of the f.e.t.s used in MOS logic with the correct circuit symbol and the simplified version usually employed for logic circuits.

## THRESHOLD VOLTAGE

The MOS device is commonly used in logic circuitry as a switch, and performs very well in this role. On resistance can be varied by the manufacturer by altering the geometry of the device, but is usually chosen to be about 10 kilohms, whereas off resistance is closer to the ideal open circuit than
can be approached with bipolar devices, and is typically $10^{11}$ ohms.

Fig. 10.3a shows a single MOS used with a discrete resistor to form a logic inverter. As the gate voltage is increased negatively, a point is reached when the device resistance drops to the on value, reducing the output voltage to a low level, which would have the effect of turning off any following stage. The actual voltage at which an MOS turns on is referred to as the "threshold voltage", and it usually lies at about 3 V . The threshold is not very abrupt, however, so this is only a nominal value.

Using conventional diffused silicon resistors in an MOS i.c. would unfortunately take up a great deal of space on the chip, losing the size advantage of the MOS active device. A diffused resistor such as is used in TTL circuits would in fact be about 1,000 times larger than a single MOS.

## MOS TRANSISTOR AS A LOAD

To sidestep this problem the arrangement in Fig. 10.3 b is employed. Here another MOS transistor is used as a load resistor, only in this case the device geometry is chosen to give an on resistance of the required 100 kilohms. The gate of this load element can either be wired permanently to the $-V_{\mathrm{Dn}}$ negative supply, holding the device permanently on, or all the gates of devices used for this purpose can be brought out to a $-V_{\text {GG }}$ common line which is held at a voltage even more negative than $-V_{\mathrm{nn}}$. This also has the effect of keeping the load on. A third alternative uses these devices as "clock-line" switches as we shall see later.

## BASIC GATE CIRCUITS

Because of the "ideal switch" characteristics of MOS, biasing problems, a feature of bipolar designs, do not arise. MOS devices are used almost as simply as relay contacts or toggle switches in gate circuits,
making them very simple to understand, once the initial unfamiliarity of the symbols is overcome.

Fig. 10.4 shows some examples of gates made with MOS alongside their relay equivalents. With this family there is no "standard" gate, both NOR and nand logic are used as it suits the designer, though it is normal practice to define gates in the negative logic convention, unlike TTL. There really seems little need to explain the action of the gates in Figs. 10.4a and 10.4 b; with the understanding of
an MOS transistor action and the relay version to refer to, readers will be able to work this out for themselves, with the knowledge of logic systems given earlier in this series.

Fig. 10.4e demonstrates how easy it is to expand MOS logic. Here two NAND gates are used in the wired-or configuration, 10 generate the AND/OR/ invert function. Interested readers may like to compare this very simple arrangement with the equivalent TTL circuitry.


Fig. 10.4a. MOS NOR configuration


Fiz. 10.4b. MOS NA.ND configuration


Fig. 10.4E MOS wired-OR :onflguration (AND/OR) INVERT]


Fig. 10.5. Static shift regiser cell and slock waveferms


Fis. 10.6. Dynamic shift register cell and clock weveform:



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|  | $2 \mathrm{NTO4}$ |
| 2 N 930 |  |
|  | -N1131 |
| 2N113: |  |
|  | $2 \mathrm{~N} 130 \%$ |
| $\because \mathrm{N} 1303$ |  |
|  | - N 1304 |
| 2 N 130. |  |
| 2 N 1304 |  |
|  | 2N $130{ }^{\circ}$ |
| -N1308 |  |
|  | $\because \mathrm{N} 1304$ |
| 2N1til: |  |
|  | $\underline{2} 1711$ |
| 2N1893 |  |
|  | 2N:147 |
| 2 N 2418 |  |
|  | $2 \mathbf{N 2 2 1 8}$ |
| 2 N 2414 |  |
|  | 2N221: |
| 2 N 29.0 |  |
|  | 2N236:4, |
| UN2483 |  |
|  | 2N2484 |
| 2 N 2904 |  |
| 2N2904A |  |
| 2N290\% |  |
|  | N290, A |


| 20p | 2 N 2904 | 80p | 40361 |
| :---: | :---: | :---: | :---: |
| 22p | 2N292\% | 22p | 4036: |
| 12p | 2N2926 | 11p | ACtoz |
| 29p | 2N3053 | 27 p | AC12 |
| 30p | 2N33..5 | 54p | AC1- |
| 40p | 2N3:03 | 13p | AC12* |
| 19p | 2N3708 | 13p | AClüd |
| 19p | - $\mathrm{NB7} 04$ | 13p | ACliti |
| 23p | 2N370. | 13p | ACI ${ }^{\text {( }}$ |
| 23p | 2 N 370 i | 13p | $\triangle \mathrm{CY}=$ |
| 33 p | 2N3707 | 13p | ADI4 |
| 33p | - $\times$ 3\%0x | 13p | AD14: |
| 38p | $\cdots \mathrm{Na7} 04$ | 13p | ADl4 |
| 36p | - $\mathrm{N}_{3} 310$ | 13p | AD161 |
| 23p | 9N3T11 | 13p | AD16.3 |
| 26 p | 2 N 3794 | 15p | AF114 |
| 54p | $\because \mathrm{N} 3904$ | 35 p | AF11, |
| 95p | 2 N 3906 | 35p | AF117 |
| 33p | 2 N 40 N | 20p | AF124 |
| 43 p | $2 \mathrm{~N}+054$ | 20p | AF127 |
| 38p | $\because \mathrm{N} 4060$ | 20p | AF134 |
| 53 p | 2N4061 | 20p | - 1239 |
| 82p | 0 N 404.2 | 20p | A8Y24 |
| 19p | 2 N 4124 | 18p | ASY:8 |
| 35p | $2 \mathrm{~N}+126$ | 27 p | BC 107 |
| 42p | 2 N 4284 | 15p | nC108 |
| 38p | $\because \mathrm{N}+28 \mathrm{Bb}$ | 15p | 1 Cl 09 |
| 42p | 2 N 428 | 15p | 13C10.3 |
| 44p | $2 \mathrm{~N}+291$ | 15p | BCl |
| 479 | 2 N 429.3 | 15p | $\mathrm{BCl}_{4}{ }^{-}$ |

## RESISTORS

| Code | Power | Tolerance | Range | ayailable | (see pote below) |  |  |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| C | 120W | $5 \%$ | $8.2 \Omega-20 \mathrm{k} \Omega$ | E12 | 7 p | ${ }^{6 p}$ | ${ }^{6 p}$ |
| C | 婁W | 5\% | $4 \cdot 7 \Omega-330 \mathrm{k} \Omega$ | E24 | 1p | 0.8p | 0.7 p |
| C | 2W | 10\% | $4.7 n-10 \mathrm{Mn}$ | E12 | 1p | 08 p | 0.7 p |
| C | $\frac{1}{2}+1$ | 5\% | $4.7 \Omega-10 \mathrm{M} \Omega$ | E 24 | 1.2 p | 1p | $0 \cdot 9 \mathrm{p}$ |
| C | 1w | 10\% | $4.7 \Omega-10 \mathrm{M} \Omega$ | E12 | 2.5p | 25p | $1.9 p$ |
| MO | ${ }_{2} \mathbf{w}$ | 2\% | 10』-1Mn | E24 | 4p | $3.5 p$ | 3p |
| WW | 1W | 10\% 1/200 | 0.22n-3.9n | E12 | 7p | 7 p | ${ }^{8 p}$ |
| WW | 3 W | 5\% | 12n-10kn | E12 | 7 p | 7 p | $6 p$ |
| WW | TW | $5 \%$ | 12, $\mathrm{l}^{10 \mathrm{k}} \Omega$ | E12 | 9p | 9p | 8p |

CODES: $\mathbb{C}$ carbon film high stability low noise, MO metal oxide Electrosil TRo ultra low noise. WW wire wound Plessey
TALUES: E12 denotes series; $10,12,15,18,22,27,33,39,47,56,68,82$ hml their decades. E24 denotes series: as E12 plus $11,13,16,20,24,30,31,43,51,62,75,91$ and their decades.

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NoT mixed volues. (Ignore fractions of 1 p on total lesistor order.)

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## SHIFT REGISTERS

MOS is rarely used to build general purpose flipflops such as the JK type, although a manufacturer's catalogue may contain a single device of this sort to enable a system to be built entirely of MOS. It is included for the sake of completeness, and it is unlikely that these devices could stand on their own merit for economic reasons.

As we have already seen, the strength of MOS lies in its ability to be produced in the LSI form, and this advantage is put to good use in the range of shift registers available. Shift registers in this family are mainly of the "serial-in/serial-out" type, and their operation may be either static or dynamic.

The static type of register uses more devices per stage than the dynamic type, but data is stored by means of cross-coupled flip-flops, and there is no minimum clock rate. Dynamic registers use the capacitor inherent in the gate construction to store data, and are not capable of storing information indefinitely as a result. A minimum clock frequency of about 1 kHz at $25^{\circ} \mathrm{C}$ is common for these registers which are used in continuously circulating applications such as delay lines.

The unit storage cells in both types of register bear little or no relation to the circuitry employed in any of the bipolar logic forms.

## STATIC REGISTER

The emphasis in MOS is on simplicity at the expense of clock circuit complexity. Fig. 10.5 shows the circuit used for a static register cell; the cross coupled flip-flop configuration is immediately apparent.

In all, three separate clock waveforms are necessary to operate this circuit, although in an LSI chip it is usual to have a circuit which generates all these from a single external timing waveform. The clock corresponds to the external waveform and $\overline{\bar{\phi}}$ fast is the $p$ clock inverted, $\bar{\phi}$ slow comes on sometime after $\bar{\psi}$ fast, and usually, although not necessarily, ends before it. Fig. 10.5 shows some typical waveforms.

A negative logic level would be transferred from the input to the gate of device A when $\phi$ comes on, and this would turn on A, pulling its output to ground. As soon as goes off, $\bar{\phi}$ fast comes on and transfers the ground on the output of $A$ to the gate of B which starts to turn off. During this operation $\bar{\phi}$ slow comes on and the rising negative at the output of B is transferred to the gate of A , holding it on. If the clock is stopped with $\phi$ off (and hence $\bar{\phi}$ fast and $\bar{p}$ slow on) data can be stored indefinitely.

The gate of an MOS transistor can be considered to be a capacitor, the insulating silicon dioxide layer acting as the dielectric, and the aluminium and silicon acting as the plates. This capacitor is of ve $y$ low value, perhaps 0.5 pF , but because of the extremely high input impedance of an MOS device any charge stored on this gate capacitor will take quite a long time to leak away. (Remember that time constant equals C times R .)

## DYNAMIC REGISTER

In the dynamic register this effect is used to store digital information, but because the charge will eventually leak away in any event, it is necessary
to quote a minimum clock frequency which is temperature dependent.

Fig. 10.6 shows the circuit of one cell of a dynamic register, and as can be seen there is no cross-coupled flip-flop, only two gated inverters. The load MOS devices are used as switches controlled by the clock, and further devices gate information between stages. The clock waveforms $\phi 1$ and $\phi 2$ are in antiphase and must not overlap.

Assuming a negative input to the cell shown, this will be stored on the gate of device A, and will turn it on as soon as the $\phi 1$ clock comes on. While $\phi 1$ is present, the output of $A$ will be pulled to ground, and this level will be gated through B to C, the gate capacitor of which will now hold a "ground" charge.
With no negative stored on its gate, C will not turn on when its load is enabled by $\$ 2$, and the output gated through $D$ will be the negative we started with delayed by one clock period.

Dynamic registers may seem pretty useless at a first glance because they cannot stand still and must keep their contents moving, but in fact there are many occasions when this is not a disadvantage.
When this is so the dynamic register has several points in its favour. First, it is about twice as fast in operation than the static type; secondly, because the loads are clocked, at low frequencies the power consumption of each cell is extremely low, typically 10 microwatts at 10 kHz . This last feature is due to the fact that power is only dissipated when the gate capacitors are charged, which makes the power consumption frequency dependent. At 1 MHz a power drain of 1 milliwatt per bit is common.

## APPLICATIONS

MOS circuits are still in their infancy, but are certain to be one of the most important advances ever to be made in the world of data processing and allied fields. Their biggest impact will be in the consumer area, and it will not be long before our homes will have the benefit of a "domestic" computer made possible by the advent of cheap MOS LSI.

A home computer could become adaptable to the telephone (which has push button dialling) so that by ringing our own number from a remote call box, and then dialling a coded message, we could instruct the computer to cook the dinner or turn on the central heating. At work the desk calculator could replace the slide rule, giving answers to all arithmetic problems at the touch of a few keys, and electronic digital test equipment such as frequency counters and digital voltmeters will shrink to pocket size.

On the way home in our car, exhaust emission will be nullified by electronic fuel injection, and the wheels will be unable to lock and skid because of another electronic system. Relaxing in our home we will be able to programme the hi fi system to sooth us in any way we fancy without leaving our armchair or sorting through piles of records.

All these things are possible now, but it will be MOS which makes them economically viable for the many.

## AVAILABLE MOS I.C.'s

Many readers may be hoping for some MOS circuits which are available to do a practical job in
amateur projects right now. Talk of dual 100 -bit shift registers in a TO-5 can will, perhaps, only interest those who like to build, or dream about, the amateur built computers of the future.

MOS circuits of simple nature are beginning to appear, and, as an example, look at a couple of Marconi-Elliott i.c.s which are intended for use in electronic organs, the MA60 and the MA70. These owo devices are housed in TO-5 cans and operate from -26 V . Inputs and outputs are compatible with DTL and TTL.

The MA60 contains six binary dividers arranged as two chains of three, each chain has three outputs, divide-by-two, four, and eight. If the two chains are used in series, a total division of 64 is obtained. The MA60 is shown in Fig. 10.7.


Fig. 10.7. Block diagram of the MA60 i.c. divider


Fig. 10.8. Block diagram of the MA70 i.c. divider


Fig. 10.9. Display programme for one character (letter H ) of the Texas read-only memory

The MA70 is rather more complex than the previous device and is intended to produce three separate semitones from a single oscillator. MA70 can be cascaded if required, and when used in conjunction with the MA60 they enable complex organs to be built on a single p.c.b. The block diagram is given in Fig. 10.8.
These are circuits available to amateurs, and they do give a hint of MOS capabilities, but to get a glimpse of advanced applications, it is necessary to return to computer and process control electronics which are finding that MOS memories are becoming increasingly attractive.

## COMPUTER MEMORY CIRCUITS

In the past the main memory in a computer has been built using ferrite core matrices, or core stores. This type of memory is of the "random access" type, as it is possible to address any location and read or write into it immediately.

Another type of memory used is the magnetic drum, which provides bulk storage but which is rather slower to address because the revolving drum may have to make a complete revolution before the correct data location is available.
Some memories are programmed during manufacture by the wiring in of diodes where data is required, these are used as fixed programmes to control computer sub-routines, or sometimes as "tables" to store constants. These memories are of the "read-only" type, and cannot be written into.

MOS LSI techniques are now being used to simulate all three of these memory systems, and the solid state versions are proving to be superior on many counts. As an example, the Texas TMS-2A-$4824-\mathrm{MH}$ read-only memory contains 2,240 bits of data which are programmed during manufacture to provide the information necessary to produce 64 alphabetical and numerical characters on a c.r.t. display.

Each character is stored as five seven-bit words which are used to modulate a dot matrix on the tube face. Fig. 10.9 shows how one of the characters is stored and formed. When a particular dot location has to be brighted up on the display a "one" is stored in the memory, each dot position is displayed in sequence, and the information to be displayed is used to address the correct character location.

This type of circuit can also be programmed to customer requirements to contain any information required, a set of sine tables for example, or a sequence programme for an industrial machine.

## DEVELOPMENTS

MOS technology is being continuously improved, and these improvements are making this type of circuit ever more easy to use.
"Silicon gate" MOS devices are now being made with threshold voltages low enough so that they can be driven directly from bipolar logic, without the need for the voltage interface circuits that were necessary with the earlier types. The silicon gate technique uses polycrystalline silicon instead of aluminium for the gate electrode, and apart from giving lower threshold voltages, this also reduces the capacitance inherent in the construction and allows higher operating speeds.
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| AF186 | 0.50 | 2Ni302-3 | 0.20 |
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| BF274 | 0.15 | Transistors |  |
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| BSY27 | 0.13 | $\mathrm{OCl}^{\mathrm{OC}}$ | 0.25 0.25 |
| BSY28 | 0.13 | - ${ }^{\circ} \mathrm{C26}$ | 0.25 0.30 |
| BSY29 | 0.13 | OC28 OC 35 | 0.30 0.25 |
| BSY95A | 0.15 | $\bigcirc$ | 0.35 |
| OC41 | 0.13 0.13 | AD149 | 0.30 |
| OC44 | 0.13 0.13 | AUY10 | 1.25 0.25 |
| $\bigcirc \mathrm{C} 71$ | 0.13 | 25034 | 0.25 |
| $\bigcirc \mathrm{C} 72$ | 0.13 | 2N3055 | 0.63 |
| $0 \mathrm{C73}$ | 0.17 | Diodes |  |
| $\bigcirc \mathrm{OCB1}$ | 0.13 | AAY42 | 0.10 |
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Germ.
B84 $100 \begin{aligned} & \begin{array}{l}\text { Silicon Diodes DO-7 glass } \\ \text { equiv. so OA200, OA202 }\end{array} \\ & \text { 50p }\end{aligned}$
$\begin{array}{ll}886 & 50\end{array}$
B88 50
IN9I4 and ING/6 min.
50p
Sil. Trans. NPN, PNP, $\quad \mathbf{5 0 p}$
equir, to OC200/1,
equiv. to BSY BSMA, etc.

| B60 | 10 | $\begin{array}{l}7 \text { Watt Zener Diodes } \\ \text { Mixed Voltages }\end{array}$ |
| :--- | :--- | :--- |
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250 mW . Zener Diodes
DO.7 Min. Glass Type
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HIO 25 Mixed volts, $\begin{aligned} & \text { Top hat type }\end{aligned}$
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The RCA COS-MOS family uses both $n$ - and $p$ channel MOS f.e.t.s on the same chip, providing circuits that will run from 5 V positive supplies with extremely low quiescent power consumption and a speed of up to 5 MHz .
The latest introduction to the MOS field is a processing system which uses low temperature doping by bombardment with ions. This process is rather complex and expensive at present but it produces circuits which will operate at the same sort of speed as TTL, a great improvement.

## PRACTICAL POINTS

MOS devices come in a wide range of package outlines, especially the more complex circuits which require large numbers of pins. Hermetically sealed packages are almost universally used, because the normal MOS chip needs to be well protected from contamination, and this rules out the simple plastic
d.i.l. packages. The TO-5 can is very popular because this style can provide enough pins, and for the more complex devices a type of ceramic d.i.l. package, or a flatpack is employed.

## PRECAUTIONS WHEN HANDLING

Because of the extremely high input impedance of the MOS, it is possible for a static charge on the gate to exceed the breakdown voltage of about 60 V , and so short out the silicon dioxide layer and ruin the device. Some circuits use protective Zener diodes to prevent this, but it is advisable to be sure by consulting the data sheet. Leakage from an unearthed soldering iron could provide the minute current necessary to destroy a device. It is often recommended that pins should be shorted together whilst in store, to prevent static build up.

## Next month: Emitter Coupled Logic (ECL)



0NE OF the extra pleasures for the electronics enthusiast going abroad is the chance to observe the effect of electronics on daily life abroad, particularly if one can stay for any length of time in a foreign household. This I was privileged to do recently-just over the channel.
It is very interesting to see high-definition French television on 819 or 625 lines and note the clarity and excellence of the picture as well as the fact that the French programme directors are as hard put as ours to fill the screen with sixty minutes of excellence per hour.
It was interesting for me to meet two French clergymen-schoolmasters, who are fervent radio amateurs, and to visit their "shacks" from where they work the world on 2 metres. Incidentally, I did not know before that for this amateur band the French authorities do not require proficiency in morse; merely the equivalent of the City \& Guilds written examination.

## APPLIED ELECTRONICS

In the line of applied electronics the Continentals are not slow to make use of the automation made possible by modern techniques. It is probably now well known that in the Renault factories most of the production of major parts, such as the boring of engine cylinder blocks, is performed and controlled by electronically based automative processes.

At the other end of the scale I recently noticed a most effective use for the light-controlled relay that has done so much to automate town-lighting systems, lift doors, car parking lights and the rest. I went into the "Messieurs" in a newly completed and finely appointed hotel in Montreux, Switzerland
and, on approaching the sanitary porcelain, noticed, coming from a metal panel in the wall, the unmistakeable "clack" of a well fed relay slamming shut. The noise coincided with a flush of clean water where it would do most good. On looking down, I noticed that my calves had interrupted a light beam aimed at a photo-cell in the side wall and, presumably, the relay thus activated had turned on a plunger-tap

## GAS LIGHTER

Another gadget 1 noticed in three separate French households I stayed in this year was a new form of gas lighter, driven direct from the mains. The lighter looks like a small, six inch long, plastic torch, with a perforated brass cap where the light bulb should be and a press-button switch on one side. When Madame wishes to light the gas ring, she takes this little "torch", applies the perforated head to the burner and presses the button. The lighter produces a noise like a rattle-snake and a bright spark inside the head immediately lights the gas.
Enquiries in two households as to how this device worked drew shrugs, no solid information, and no enthusiasm in response to my wish to take it to pieces. Finally, in the third family I met sympathyfrom the clergyman ham, who affirmed that it worked like an electric bell, but was dissuaded from dismantling it there and then by his sister, who kept house for him. However, I was later able to obtain such a lighter, and no sooner had I returned to my home den than 1 took it to pieces and found that it does, indeed, work like an electric bell, as my friend had said.
The d.c. resistance of the coil in the specimen examined was 150 ohms, wound from 42 s.w.g. wire. At 230 volt mains a current of about 1.5 amp is broken at the contact bosses and for such slender wire, the sheer temerity of the concept might at first appear alarming. It must be remembered, however, that with such a healthy spark the gas is lit immediately, so that the button switch is released after a few seconds and no fuses blow.
Anyway, these lighters are in use in thousands of French homes, are on general sale at the equivalent of approximately $37 \frac{1}{2} p$ each and their construction must therefore be presumed to have the approval of Electricite de France, the central electricity authority of France.


## TAPE RECORDERS

H. W. Hellyer<br>Published by Fountain Press<br>239 pages, $8 \frac{1}{2}$ in $\times 5 \frac{1}{2} \mathrm{in}$. Price $\mathbf{E} 2.25$ (45s)

MRITten by the author of the Tape Recorder Servicing Manual, this, in like vein, is an essentially practical book that sets out to educate the reader painlessly into tape recorder techniques and simple maintenance.

From an opening chapter sketching the birth, development and growth prospects, the author embarks on a very readable breakdown on machine principles, naming of parts and functions, all being punctuated with some valuable workshop observations.

Guidelines to recorder and microphone choice will no doubt appeal to prospective buyers although it seems, the yardstick axiom of "You only get what you pay for" must eternally prevail.

Chapters on maintenance for both tape and deck are very well illustrated. A final chapter on tests and measurements embraces choice of service equipment, bench tips and typical measurement hook-ups for determining wow and flutter, distortion levels and signal to noise ratios, etc.

All in all, a must for any user of tape recorders, as it affords a useful reference that is very easily dipped into.

## FOUNDATIONS OF WIRELESS AND ELECTRONICS Eighth edition

## By M. G. Scroggie B.Sc., C.Eng., F.I.E.E. Published by Iliffe Books <br> 521 pages, $8 \frac{3}{2}$ in $\times 5 \frac{1}{2} \mathrm{in}$. Price 63 ( $60 \mathrm{~s}^{\circ}$ )

THERE must be thousands who have built their hobby, or even their career, upon Mr. M. G. Scroggie's "Foundations". First published in 1936, this well known work has re-appeared in new editions from time to time. The present edition, the eighth, is noteworthy for the addition of "electronics" to the title. This is justified by the inclusion of two new chapters providing brief but useful accounts of such subjects as waveform generators and computers.

Apart from this extension of its range, the general character and arrangement of the book has not changed over much, and wireless transmission and reception remains the dominant theme. But much of the material has been completely re-written, and semiconductors have now nearly, but not entirely, ousted thermionic valves.

Those not already familiar with Mr. Scroggie's classic can be assured that no previous knowledge of radio or electronics is assumed. The text excels in clarity and exposition, and there is little demand upon mathematics. Starting with first principles of electricity and circuit elements, the book proceeds to electronic devices, both thermionic and semiconductor, and explains their function in straightforward descriptive terms. Only in chapter 12 does the going become tough (as the author warns the reader) when transistor and valve equivalent circuits are evolved. Full understanding of this chapter is not, however, vital at the elementary stage.

The application of all the foregoing principles is demonstrated with stage by stage description of the various processes involved in a radio communications system. The principles of cathode ray tubes, television and radar are also outlined.

The two new chapters provide a sound, concise introduction to the many other uses of electronics which stem mainly from pulse switching techniques, as distinct from the generation, detection, and amplification of sinusoidal signals.
F.E.B.

## RADIO VALVE AND TRANSISTOR DATA

## Compiled by A. M. Ball

Published by Butterworth \& Co. Ltd.
232 pages, $10 \frac{3}{4}$ in $\times 8 \frac{1}{4} \mathrm{in}$. Price $\mathbf{C 0 . 7 5}$ (15s)

Substantially revised and added to, this is the ninth edition of a very popular reference on valve and semiconductor electrical characteristics.

Additions to the previous contents list are colour tubes, f.e.t.s, tunnel diodes and i.c.'s, the latter including both digital and linear references.

Full marks must be given for the choice of a larger type face in the data presentation. This has meant, inevitably, some considerable pruning in obsolete device information, so don't just throw away that older edition as it will prove to be a valuable complement.

I suppose that in a work of this nature, errors can occur, but those that I found are inexcusable.

In the Amplifier Triodes section, the headings $\mathrm{gm}_{\mathrm{m}}$ and $r_{a}$ should be transposed. The data for the PCC89 given in the Mullard Valve Data Book includes the description "Variable-mu frame-grid double triode".

In the Integrated Circuits section, the pin layout diagrams (p.199) do not include identification of mode connections. If one has to refer to manufacturers' data for this, then there was little point in including the technical data. It should also be made clear which view is shown in the drawings.

Finally, it would be very much easier to locate transistor types on the data pages if some semblance of alphabetical order were adopted.
G.G.

## BEGINNERS GUIDE TO RADIO Seventh Edition

## By Gordon J. King <br> Published by Newnes-Butterworths <br> 194 pages. $7 \frac{1}{2}$ in $\times 5$ in. Price $\& 1$

THIS book is an updated version of an original of the same title by F. J. Camm, it is not just a rewrite in parts but a completely new book. The author's explanations of the basic principles are excellent and this book would prove useful to all studying electronics as well as basic radio. It is unfortunate that most of the work is based on valve theory and practice, however the radio principles are unaffected by this and there is a useful section on transistor theory and function and some transistor circuits are given and described in the text.

Sections 11 and 12 are concerned with "Disc Record Players and Radiograms" and "Hi-Fi Reproduction". Although these items may seem rather out of context under the title of this book they are both worthwhile sections describing the principles involved and giving block diagrams of the systems.

A selection of circuit symbols is given at the front of the book together with a brief description of each and lists of abbreviations and a wavelength/frequency conversion table are given at the back. Also included is an index of words and terms described in the text.
M.K.

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changeable with 2.30 s in all applications).
Power Outputs
Z.30 15 watts R M.S. into 8 ohms using 35 volts: 20 watts R M S. Mito 3 ohms using 30 volts.
Z.50 40 watts R.M $S$ into 3 ohms using 40 volts: 30 watts R.M S. into 8 ohms. using 50 volts.
Frequency response: 30 to $300000 \mathrm{~Hz} \pm 1 \mathrm{~dB}$.
Distortion: $002 \%$ into 8 ohms.
Signal to noise ratio: better than 70 dB unweighted.
Input sensitivity: 250 mV into 100 Kohms.
For speakers from 3 to 15 ohms impedance.
Size $3 \frac{1}{2} \times 2 \frac{1}{d} \times \frac{1}{2} \mathrm{in}$.
2.30

Built tested and guaranteed with circuits and instructions manual
£4.48
2.50

Bult. tested and guaranteed with circurts and instructionsmanual. $£ 5.48$

## Power Supplv Units



Designed specially for use with the Project 60 system of your chorce.
Illustration shows PZ. 5 to left and PZ. 8 (for use with Z .50 s ) to the right. Use PZ .5 for normal $Z .30$ assemblies and PZ. 6 where a stablised supplv is essential.
PZ-5 30 volts unstabilised £4.98
PZ $\mathbf{6} 35$ volts stabt/ised $\mathbf{£ 7 . 9 8}$
PZ-8 45 volts stabilised
(less marns transtormer) $£ 7.98$
PZ-8 mains transformer $£ 5.98$

Stereo 60
pre-amp/control unit


Designed for the Project 60 range but suitable for use with any high quality power amplifier. Agaın silicon epitaxial planar transistors are used throughout. achieving a really high signal-to-noise ratio and excellent tracking between channels. Input selection is by means of push buttons and accurate equalisation is provided for all the usual inputs.

## SPECIFICATIONS

Input sensitivities: Radio-up to 3 mV . Mag. p.u. 3 mV : correct to R.I.A.A. curve $\pm 1 \mathrm{~dB}: 20$ to 25.000 Hz . Ceramic p.u.-up to 3mV: Aux-up to 3 mV .
Output: 250 mV
Signal-to-noise ratio: better than 70 dB .
Channel matching: within 1 dB
Tone controls: TREBLE +15 to -15 dB a: $10 \mathrm{KHz}:$ BASS +15 to -15 dB at 100 Hz .
front panel: brushed aluminium with black knobs and controls.
Size: $8 \frac{1}{4} \times 1 \frac{1}{2} \times 4$ ins.
Built, tested
andguaranteed.

## £9.98

## Active Filter Unit



For use between Stereo 60 unit and two Z. 30 s or $Z .50 \mathrm{~s}$, and is easily mounted. It is unique in that the cut-off frequencies are continuously variable. and as attenuation in the rejected band is rapid ( $12 \mathrm{~dB} /$ octave), there $: 5$ less loss of the wanted signal than has previously been possible. Amplitude and phase distortion are negligible. The A.F.U. Is suitable for use with any other amplifier system. Two stages of filtering are incorporated rumble (high pass) and scratch (low pass). Supply voltage - 15 to 35 V . Current - 3 mA . H.F. cut-off $(-3 \mathrm{~dB})$ variable from 28 kHz to 5 kHz . L.F cut-off $(-3 \mathrm{~dB})$ variable from 25 Hz to 100 Hz . Distortion at $1 \mathrm{kHz}(35 \mathrm{~V}$. supply) $0.02 \%$ at rated output.
Built, tested
and guaranteed
£5.98

## Stereo FM Tuner



## first in the world to use the

phase lock loop principle
Before production of this tuner. the phase lock loop principle was used for receiving signals from space craft because of its vastly improved signal to noise ratio over other systems. Now. for the first time, the principle has been applied to an FM tuner with fantastically good results. Other original features include vartcap diode tuning, printed circuit colls, an I.C. in the specially designed stereo decoder and squelch circuit for silent tuning between stations. Senstivity is such that good reception becomes possible in difficult areas. Foreign stations can be tuned in suitable conditions and often a few inches of wire are enough for an aerial. In terms of a high fidelity this iuner has a lower level of distortion than any other tuner we know. Stereo broadcasts are received automatically as the tuning control is rotated. a panel indicator lighting up as the stereo signal is tuned in. This tuner can also be used to advantage with any other high fidelity system.

## SPECIFICATIONS:

Number of transistors: 16 plus 20 in I.C
Tuning range: 87.5 to 108 MHz
Capture ratio: 1.5 dB
Sensitivity: $2 \mu \mathrm{~V}$ for 30 dB quieting: $7 \mu \mathrm{~V}$ for full limiting.
Squelch level : $20 \mu \mathrm{~V}$.
A.F.C. range: $\pm 200 \mathrm{KHz}$

Signal to noise ratio: $>65 \mathrm{~dB}$
Audio frequency response: $10 \mathrm{~Hz}-15 \mathrm{KHz}$ $( \pm 1 \mathrm{~dB})$
Total harmonic distortion: $0.15 \%$ for 30\% modulation
Stereo decoder operating level: $2 \mu \mathrm{~V}$
Pilot tonesuppression: 30 dB
Cross talk: 40 dB
Cross talk: 40 dB
Output voltage: $2 \times 150 \mathrm{mV}$ R.M.s
Aerial Impedance: 750 hms
Indicators: Mains on: Stereo on; tuning indicatop
Operating voltage: $\mathbf{2 5 - 3 0}$ VDC
Size: $3.6 \times 1.6 \times 8.15$ inches: $91.5 \times 40 \times 207 \mathrm{~mm}$


Price: $\mathbf{P} 25$ built and tested. Post free

## Guarantee

If within 3 months of purchasing Progect ' 60 modules directly from us, you are dissatisfied with them. we will refund your money al once. Each module is guaranleed ro work pe tectly and should any defect alise in normal use we will service $t$ at once and without any cost to you whatsoever provided that it is returned to us within 2 years of the purchase date. There will be a smatl charge for service thereafter No charge for postage by surface mall. Air-mall charged at cost.

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Name

Address

## Sinclair IC10/Q16/Micromatic

IC10


The world's most advanced high fidelity amplifier
This is the world's first monolithic integrated circuit high fidelity power amplifier and preamplifier. The circuit itself is a chip of silicon only a twentieth of an inch square by one hundredth of an inch thick, having 5 watts RMS output ( 10 watts peak). It contains 13 transistors (including two power types). ? diodes, 1 zener diode and 18 resistors, and is encapsulated in a solid plastic package which holds the metal heat sink and connecting pins. This exciting device is more rugged and has considerable performance advantages. including complete freedom from thermal runaway and a very low level of distortion. The IC10 is primarily intended as a full performance high fidelity power and preamplifier, for which application it only requires the addition of such components as tone and volume controls and a battery or mans power supply. It may also be used in other applications including car radios. electronic organs. servo amplifiers (it is dc coupled throughout) etc.
Circuit Description
The first three transistors are used in the pre-amp and the remaining 10 in the power amplefier. Class $A B$ output is used with closely controlled quiescent current which is independent of temperature. There is generous negative feedback round both sections and the amplifier is completely free from crossover distortion at a!l supply voltages. making battery operation eminently satisfactory.
Each IC1O is sold with a comprehensive manual giving circuit and wiring diagrams for a large number of applications in addition to high fidelity. These include oscillators, etc. The pre-amp section can be used as an RF or IF, amplifier without any additional transistors.

## Specifications:

Output: 10 watts peak. 5 watts RMS continuous Frequency response: 5 Hz to $100 \mathrm{kHz} 1 \pm \mathrm{dB}$. Total harmonic distortion: Less than $1 \%$ at full output.
Load impedance: 3 to 15 hms .
Load impedance: 3 to 15 ohms.
Power gain: 110 dB ( $100,000,000,000$ times) total.
Supply voltage: 8 to 18 volts. (A Sinclair power unit, PZ. 7 is available for mains operation).
Size: $1 \times 0.4 \times 02$ in plus heat sink and tags Sensitivity 5 mV .
Input impedance: Adjustable externaliy up to 2.5 Mohms.

Price (with manual)• 59/6 (£2.97⿺) post free.

Q16


## High fidelity loudspeaker

The 016 employs the well proven acoustic principles specially developed by Sinclair in which a special driver assembly is meticulously matched to the characteristics of the uniquely designed cabinet. In reviewing this exclusive Sinclaır design, technical journals have justly compared the 016 with much more expensive loudspeakers. Its shape enables the 016 to be positioned and matched to its environment to much better effect than is the case with conventionally styled enclosures. A solid teak surround with a special all-over cellular foam front is used as much for appearance as its ability to pass all audro frequencies.

This elegantly designed shelf mounting speaker brings genuine high fidelity within reach of every music lover.

## Specifications:

Construction: Special sealed seamless sound or pressure chamber with internal baffle.
Loading: up to 14 watts TMS
Input impedance : 8 ohms
Frequency response: From 60 to 16.000 Hz . confirmed by independently plotted B and K curve. confirmed by independently plotted $B$ and $K$ curve.
Driver unit: Special high compliance unit having Driver unit: Special high compliance unit having
massive ceramic magnet of 11,000 gauss, aluminium massive ceramic magnet of 11,000 gauss, aluminium
speech coll and a special cone suspension for speech coll and a specia
excellent transient response.
Size and siyling: 9a in square on face $\times 4 \frac{\mathrm{in} \text {. deep }}{}$ with neat pedestal base. Black all-over cellular foam front with natural solid teak surround.
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Micromatic


## Britain's smallest radio

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## Specifications:

Size: $36 \times 33 \times 13 \mathrm{~mm}\left(14 / 5 \times 13 / 10 \times \frac{1}{2} \mathrm{~m}\right.$.)
Weight : including batteries. $28.4 \mathrm{gm}(1 \mathrm{oz}$.$) .$
Case: Black plastic with anodised alumınium front panel and spun aluminium dial.
Tuning: medrum wave band with bandspread at higher frequencies, ( 550 to 1.600 Hz ).
Earpiece: Magnetic type.
On/off switching: By inserting and withdrawing earpiece plug.
Kit in pack with earpiece. case, instructions and Kit in pack with oar
solder $49 / 6\left(\mathrm{f} 247 \frac{1}{2}\right)$.
Ready built, tested and guaranteed, with earpiece 59/6 (£2.97t).
Two Mallory Mercury batteries type RM675 required. From radio shops, chemists, etc.

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## HARVERSONIC SUPER SOUND 10 + 10 STEREO AMPLIFIER KIT <br> $0 \cdot 0$

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A really first-clags Hi-Fi stereo Amplifler Kit. Tise 14 transistora iacluding Sillicon Transiators in the frrst five stages on each chasne! resulting in even lower noise with Basa, Treble and two Volume Controlated Suithole for use with Ceraninic or Crystal cartriugcs. Output stage for any speakers from 5 to la ohms. Conpact lesign, all parts supplied including alrilled metal work, high quality ready dilled printed circuit board, ateractive front panel, finohs, wire, solder. nuts, holtg- no extris to buy. Sinple step by step instructions enable any constructor to build an amplifier to be proul of. Brief ${ }_{5}$ specincatmit: Power output 14 r.m.s. per channel into Sensitivits, Frequency response -'3d73 $12-30,000 \mathrm{~Hz}$. wldth $\ddagger 315312-15.000 \mathrm{~Hz}$. Hass hoost approx, to a Treble cut approx. © -16 AB .: Negative feedlack $18,1 \mathrm{~B}$ over main amp. Fower requirements $3 \dot{5} \mathrm{~V}$ at 1.0 amp. Overall size- $12^{*}$ wide $8^{*}$ lleep ${ }^{23}{ }^{3 *}$ high. Fully detailed 7 -pare construction minuat atind garts list ree with kit or seld 1 Rp plus large R.A.t.
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Generous size Driver and Output Tranaformers. Outpat transformer tapped for 3 ohin and 15 ohm apeakers.
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$\mathrm{BP} 41=7441$
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$\mathrm{BP} \overline{\mathrm{z}} 3=74 \overline{\mathrm{z}} 3$
$\mathrm{BP} 54=7454$
BP 60
$=7460$
$\mathrm{BP70}=7470$


| $\mathrm{BP73}=7473$ |
| :--- |
| BP 4 |
| 7474 |


| $\mathrm{BP74}=746$ |
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| BP75 |
| BP 76 |
| 147 |

$\mathrm{BP75}=747,5$
$\mathrm{BP76}=7476$
BP80 $=7480$
$\mathrm{BP81}=7481$
$\mathrm{BPB2}=7482$
$\mathrm{BP83}=7483$
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$\begin{aligned} \mathrm{BP92} & =7492 \\ \mathrm{BP93} & =7493\end{aligned}$
$\mathrm{BP93}=7493$
$\mathrm{BP94}=7494$

| $\mathrm{BP94}$ |
| :--- |
| BP 95 |
| $=7495$ |

$\mathrm{BP96}=7496$
$\mathrm{BP} 100=7+100$ BP118 $=74118$ $\mathrm{BP121}=74121$ BP141 $=74141$ $\mathrm{BP140}=74150$ $\mathrm{BP}_{163}=74101$
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## 60 Mi ed germanium transist ors $\boldsymbol{A} \mathbf{F} / \mathbf{R F}$

Ti．Germanium gold bonded diodes sim．O．AJ，O．14
40 Cermanium transistors like OC8।，（c＇I？8
fi0 200 ma sub－min．Sill diorles
30 Silicon planar transistors NPN mim．BsY95A．2N70
1f Silicon rectifiers Top－Hat 7.00 mA up to 1,0001

$\therefore 0$ Mixed volts 1 watt Zener dionde
30 PNP silicon planar transistors To－$\overline{\mathrm{J}}$ sim． 1 Nitl ：
30 PNP－NPN sil．transistors Ot＂200 \＆： 24104
wo Mixet silicon and germanium tiodes
2．5 NPN silieon planar transistors TO－ 5 sinu． 2 N 697 103 －Anp silicon rectiflers athal type up to 1000 PIV
30 Germanium PNP AF transistors TO－Jlike ACY I 8 b－Imps siticon rectiflers 13 YZ 13 tyrue up to 600 PI Silicon NPN transislors like BC108

 30 Malt＇s like MAT＇series f＇Nl＇transistors

 30 Fust awitching silicon tionles fike 1 NO I 4 miero－min Finperimenters＇assurtment of integrated circuitn，untestent
 $\because 0 \mathrm{Sil}$ ．Planar Nf＇N trath，low nuise artp $\because \mathrm{N} 370{ }^{-}$

Zener dionles 400 mW Doi case mined volta， 3 －is
jú Plastic case I ank silicon rectiliets IN 4000 series

25 Sill planar trans．PNP TO－18 2 N 290 t

30 Sil．alloy trans．SO－2 PNP，Otw00 $2 \mathrm{~S} 3 \cdots$
30 Fast switching sil．trans．NPN， $400 \mathrm{Mc} / \mathrm{s} \because \mathrm{N} 3011$
30 Rド germ，PNP trans．※N13035；TO－
U40 10 Dual trang．\＆Ican TO－5 $\mathrm{N}=040$
U41 $\xrightarrow{3} \mathrm{RF}$ germ．trans．To－1 OCA5 NKTz：

Corle Nos．mentioned above are given as a guide to the type of levice in the Pak．The derices themselves are normally mumarked

NEW QUALITY TESTED PACKS Pack Description

|  | ${ }^{0} 0$ Jied sput（rans．PNP |
| :---: | :---: |
| Q2 | 16 White spot R．F．trans．PNP |
| Q3 | 40 C 77 type trang． |
| Q4 | is Matcheil trans．OC44／45／81／815 |
| Qu | $40 \mathrm{C7} \mathrm{j}^{\text {dransiators }}$ |
| Q6 | 40 OC 2 transistors |
| Q7 | 4 ACl28 trans．PNP high gain |
| Q8 | 4 ACLO6 trans．PNP |
| （29 | 7 OC81 type trans． |
| Q10 | 70071 type trans． |
| Q11 | $\because$－${ }^{\text {Cl127／128 }}$ comp．pairs |
| Q13 | 3 AF116 type trans． |
| Q13 | 3 AFII type trans． |
| Q14 | 3 OC171 H．F．type trans． |
| Q15 | 二 $2 \mathrm{~N} \geq 92 \mathrm{fj}$ sil．epoxy trans． |
| Q1／ | ${ }^{3}$ GET880 low noise germ．tran |
| Q17 | 3 NPN 1 ST141 \＆STIL40 |
| Q18 | 4 Madt＇s＂Mat 100 \＆ 2 MAT 100 |
| Q19 |  |
| Q20 | 4 OC 44 germ trans A．F． |
| Q2 ${ }^{1}$ | 3 AC127 NPN germ．trans． |
| Q ${ }^{3} \cdot \underline{2}$ | 20 NKT trans．A．F．R．F．coden |
| Q23 | 10 OA：202 sil．diodes sub－ |
| Q24 | ＊O．s81 diodes |
| Q：3 |  |
| Q：6 | 80.495 germ．diodea sub min． 1 N 69 |
| Q27 | $\because 10 \mathrm{~A} 600 \mathrm{PlV}$ sil．rects， $\mathrm{J84} 5 \mathrm{R}$ |
| Q 28 | $\because$ Bil．power rects．BYZ13 |
| Q29 |  $1 \times 3 \mathrm{~N} 698$ |
| Q30 | 7 \＄il．awitch trans． $2 \mathrm{~N} / 06 \mathrm{NPN}$ |
| Q31 | 6 Sil．switch trang．2N708 NPN |
| Q32 | $\begin{aligned} & 3 \text { PNY sil trans } \because \times 2 \times 1131 \text {, } \\ & 1 \times x \text {. } \end{aligned}$ |
| Q33 | 3 Eil NPN trans．${ }^{\text {N }}$ N1711 |
| Q34 | 7 Sil．NPN trans． 2 No360，b004HZ． |
| Q3 | $3 \text { Sil. PNP TO }$ |
| Q310 | 7 NP 3646 TO－18 plastic 300 MH ？ |
| Q 37 | 3 N 3003 NPN ail．trans． |
| Q3\％ | 7 PNP trana $4 \times 2 \mathrm{~N} 3703,3 \times 2 \mathrm{~N} 3 \mathrm{O} 0$ |
| Q34 | 7 NPN trans． $4 \times 0$ N3704， $3 \times 2 \mathrm{~N} 370.7$ |
| Q40 | 7 NPN amp， $4 \times 2$ N3707， $2 \times 3 \mathrm{~N} 3708$. |
| Q 41 | 3 Plastic ${ }^{\text {N }}$＇${ }^{\text {N TO－18 }}$ |
| Q4를 | 6 NPN trans． 2 Nut 2 |
| Q43 |  |
| Q44 | 7 NPN 1 rans， $4 \times$ BC108， $3 \times 1 \mathrm{CO} 09$ |
| Q4J | $3 \mathrm{BCl13} \mathrm{NPN}$ TO－18 trans． |
| Q46 | 3 BCH 1 J N PN TO－utrans． |
| Q4 ${ }^{-}$ | fi NPN high gain $3 \times \mathrm{BC167,3} \mathrm{\times 13} \mathbf{C 1 5}$ |
| Q48 | 4 BCY 70 NPN trans．TO－18 |
| 249 |  |
| Qio | T BSY 28 NPN Bwitch T0－18 |
| Q 01 | 7 B8Y90̈A NPN trans 300MI |
| Qit | B BY100 type ail．rect． |
| Qu3 | A．：Sil．germ．trans．mixed all marked mew |

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