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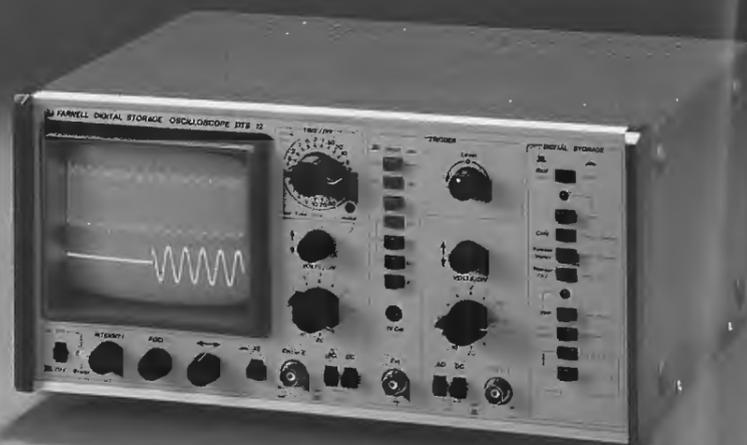
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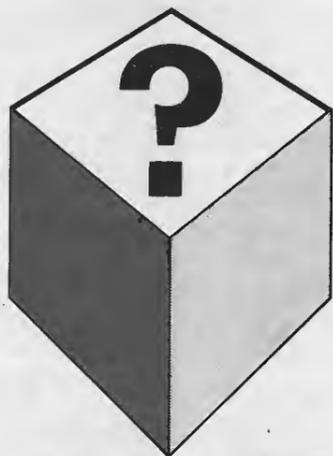
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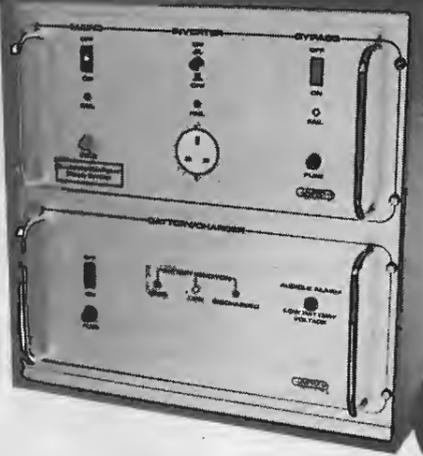
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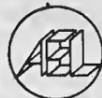
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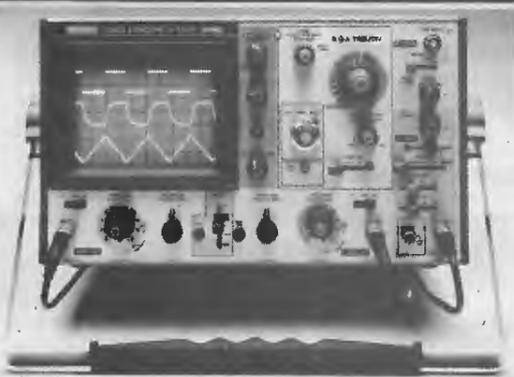
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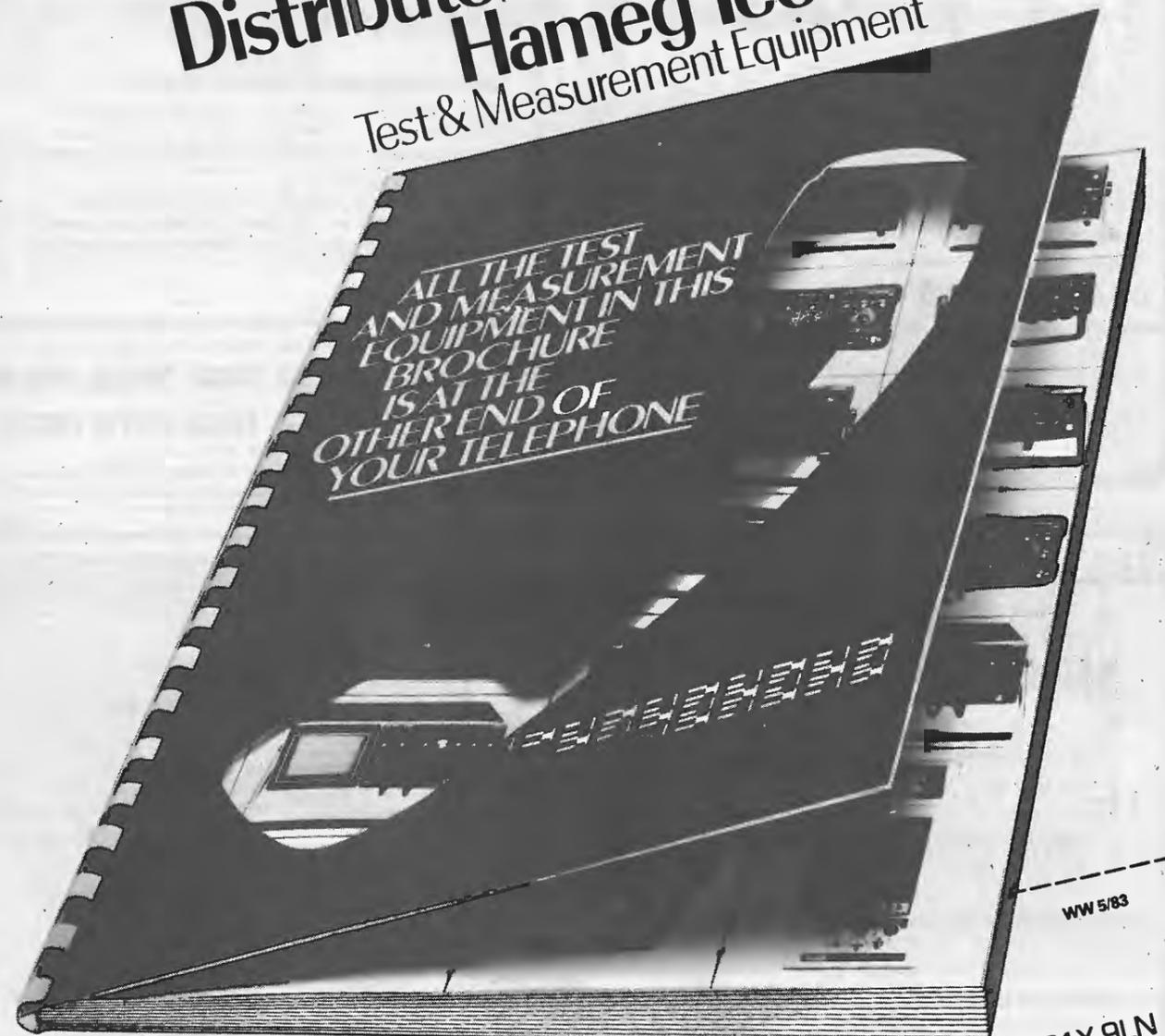
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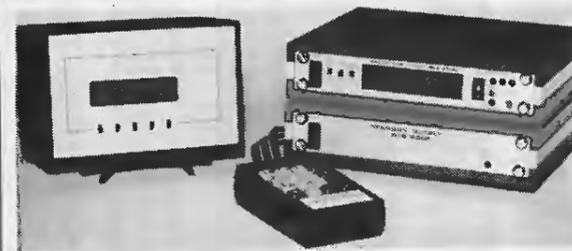
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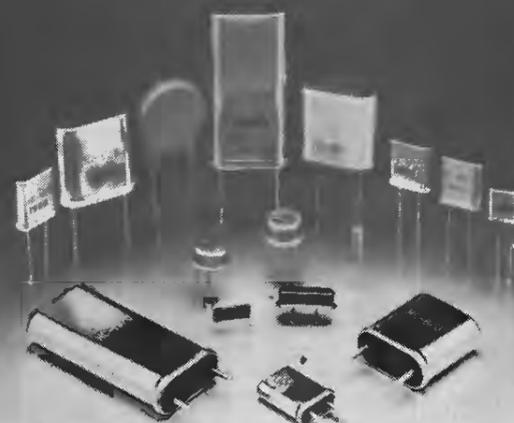
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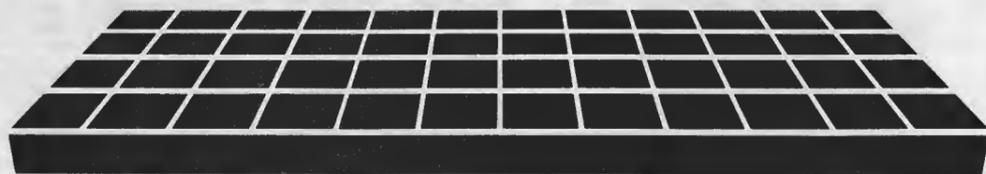
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### Specifications (Direct Output): BGW Model 620B

**OUTPUT POWER:**  
200 watts minimum sine wave continuous power output per channel with both channels driving 8-ohm loads over a power band from 20Hz to 20kHz. The maximum Total Harmonic Distortion at any power level from 250 milliwatts to 200 watts shall be no more than 0.25%.  
1kHz Power: 240 watts into 8 ohms per channel, both channels operating, 0.25% Total Harmonic Distortion.

Intermodulation Distortion:	Less than 0.06% from 250 milliwatts to rated power.
Small Signal Frequency Response:	+0, -3dB, 1Hz to 70kHz.
Hum and Noise Level:	Better than 100dB below 200 watts (unweighted, 20Hz to 20kHz).
Damping Factor:	Greater than 120 to 1 at 8 ohms and 1kHz.
D.C. Offset Voltage:	Less than 10 millivolts (at output terminals).
Load Impedance:	Designed for any load impedance equal to or greater than 4 ohms.



### Specifications (Direct Output): BGW Model 320B

**OUTPUT POWER:**  
100 watts minimum sine wave continuous average power output per channel with both channels driving 8-ohm loads over a power band from 20Hz to 20kHz. The maximum Total Harmonic Distortion at any power level from 250 milliwatts to 100 watts shall be no more than 0.2%.  
1kHz Power: 105 watts into 8 ohms per channel, both channels operating, 0.2% Total Harmonic Distortion.

Intermodulation Distortion:	Less than 0.05% from 250 milliwatts to rated power.
Small Signal Frequency Response:	+0, -3dB, 1Hz to 50kHz.
Hum and Noise Level:	Better than 100dB below 100 watts (unweighted 20Hz to 20kHz).
Damping Factor:	Greater than 150 to 1 at 8 ohms and 1kHz.
D.C. Offset Voltage:	Less than 10 millivolts (at output terminals).
Load Impedance:	Designed for any load impedance equal to or greater than 4 ohms.



For further information on these and other BGW amplifiers, contact Nikki Antoniou, Theatre Projects, 10 Long Acre, London WC2E 9LN, Tel. 240 5411

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## EP4000 EPROM EMULATOR PROGRAMMER



The microprocessor controlled EP4000 will emulate and program all the popular EPROMs including the 2704, 2708, 2716(3), 2508, 2758, 2516, 2716, 2532 and 2732 devices. Personality cards and hardware changes are not required as the machine configures itself for the different devices. Other devices such as bipolar PROMs and 2764 and 2564 EPROMs are programmed with external modules.

The editing and emulation facilities, video output and serial/parallel input/output provided as standard make the EP4000 very flexible to allow its use in three main modes:

- As a stand alone unit for editing and duplicating EPROMs.

Items pictured are: ● EP4000 Emulator Programmer - £545 + £12 delivery; ● BSC buffered simulator cable - £39; ● MESA 4 multi EPROM simulator cable - £98; ● 2732A Programming adaptor - £39; ● 2764 Programming adaptor - £64; ● 2564 Programming adaptor - £64; ●

- As a slave programmer used in conjunction with a software development system or microcomputer.
- As a real time EPROM emulator for program debugging and development (standard access time of the emulator is 300ns).

Data can be loaded into the 4k x 8 static RAM from a pre-programmed EPROM, the keypad, the serial or parallel ports and an audio cassette. Keypad editing allows for data entry, shift, move, delete, store, match and scroll, and a 1k x 8 RAM allows temporary block storage. A video output for memory map display, as well as the built-in 8 digit hex display allows full use of the editing facilities to be made.

BP4 (TEXAS) Bipolar PROM Programming module - £190

Also available (not shown): ● VM10 Video monitor - £99; ● UV141 EPROM Eraser with timer - £78; ● GP100A 80 column Printer - £225; ● PI100 interface for EP4000 to GP100A - £65.

*VAT should be added to all prices*

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2704  
2708  
2716(3)  
2508  
2758A  
2758B  
2516  
2716  
48016  
2532  
2732  
2732A  
68732-0  
68732-1  
68766  
68764  
2764  
2564  
MK2764

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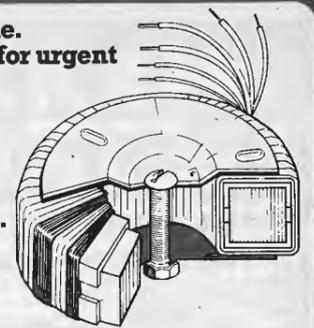
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<b>NEW!</b>	<b>NEW!</b>	<b>NEW!</b>												
15 VA 62 x 34mm 0.35Kg Regulation 19%	0x010 0x011 0x012 0x013 0x014 0x015 0x016 0x017	6+6 9+9 12+12 15+15 18+18 22+22 25+25 30+30	1.25 0.83 0.63 0.50 0.42 0.34 0.30 0.25	<b>£5.12</b> + p & p £0.78 + VAT £0.89 TOTAL £6.79	120 VA 90 x 40mm 1.2Kg Regulation 11%	4x010 4x011 4x012 4x013 4x014 4x015 4x016 4x017 4x018 4x028 4x029 4x030	6+6 9+9 12+12 15+15 18+18 22+22 25+25 30+30 35+35 110 220 240	10.00 6.66 5.00 4.00 3.33 2.72 2.40 2.00 1.71 1.09 0.54 0.50	<b>£7.42</b> + p & p £1.72 + VAT £1.37 TOTAL £10.51	300 VA 110 x 50mm 2.6Kg Regulation 6%	7x013 7x014 7x015 7x016 7x017 7x018 7x025 7x028 7x033 7x029 7x030	15+15 18+18 22+22 25+25 30+30 35+35 40+40 45+45 50+50 110 240	10.00 8.33 6.82 6.00 5.00 4.28 3.75 3.33 3.00 2.72 1.36 1.25	<b>£10.88</b> + p & p £2.05 + VAT £1.94 TOTAL £14.87
30 VA 70 x 30mm 0.45Kg Regulation 18%	1x010 1x011 1x012 1x013 1x014 1x015 1x016 1x017	6+6 9+9 12+12 15+15 18+18 22+22 25+25 30+30	2.50 1.66 1.25 1.00 0.83 0.68 0.60 0.50	<b>£5.49</b> + p & p £1.10 + VAT £0.99 TOTAL £7.58	160 VA 110 x 40mm 1.8Kg Regulation 8%	5x011 5x012 5x013 5x014 5x015 5x016 5x017 5x018 5x026 5x028 5x029 5x030	9+9 12+12 15+15 18+18 22+22 25+25 30+30 35+35 40+40 110 220 240	8.89 6.66 5.33 4.44 3.63 3.20 2.66 2.28 2.00 1.45 0.72 0.66	<b>£8.43</b> + p & p £1.72 + VAT £1.52 TOTAL £11.67	500 VA 140 x 60mm 4Kg Regulation 4%	8x016 8x017 8x018 8x026 8x025 8x033 8x042 8x028 8x029 8x030	25+25 30+30 35+35 40+40 45+45 50+50 55+55 110 220 240	10.00 8.33 7.14 6.25 5.55 5.00 4.54 4.54 2.27 2.08	<b>£14.38</b> + p & p £2.40 + VAT £2.52 TOTAL £19.30
50 VA 80 x 35mm 0.9Kg Regulation 13%	2x010 2x011 2x012 2x013 2x014 2x015 2x016 2x017 2x028 2x029 2x030	6+6 9+9 12+12 15+15 18+18 22+22 25+25 30+30 110 220 240	4.16 2.77 2.08 1.66 1.38 1.13 1.00 0.83 0.45 0.22 0.20	<b>£6.13</b> + p & p £1.35 + VAT £1.12 TOTAL £8.60	225 VA 110 x 45mm 2.2Kg Regulation 7%	6x012 6x013 6x014 6x015 6x016 6x017 6x018 6x026 6x025 6x033 6x028 6x029 6x030	12+12 15+15 18+18 22+22 25+25 30+30 35+35 40+40 45+45 50+50 110 220 240	9.38 7.50 6.25 5.11 4.50 3.75 3.21 2.81 2.50 2.25 2.04 1.02 0.93	<b>£9.81</b> + p & p £2.05 + VAT £1.78 TOTAL £13.64	625 VA 140 x 75mm 5Kg Regulation 4%	9x017 9x018 9x026 9x025 9x033 9x042 9x028 9x029 9x030	30+30 35+35 40+40 45+45 50+50 55+55 110 220 240	10.41 8.92 7.81 6.94 6.25 5.68 5.68 2.84 2.60	<b>£17.12</b> + p & p £2.55 + VAT £2.95 TOTAL £22.62
80 VA 90 x 30mm 1Kg Regulation 12%	3x010 3x011 3x012 3x013 3x014 3x015 3x016 3x017 3x028 3x029 3x030	6+6 9+9 12+12 15+15 18+18 22+22 25+25 30+30 110 220 240	6.64 4.44 3.33 2.66 2.22 1.81 1.60 1.33 0.72 0.36 0.33	<b>£6.66</b> + p & p £1.72 + VAT £1.26 TOTAL £9.64										

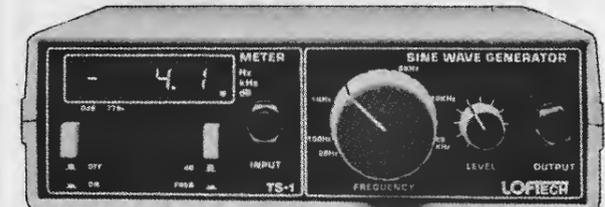
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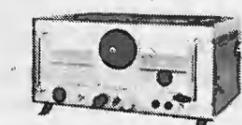
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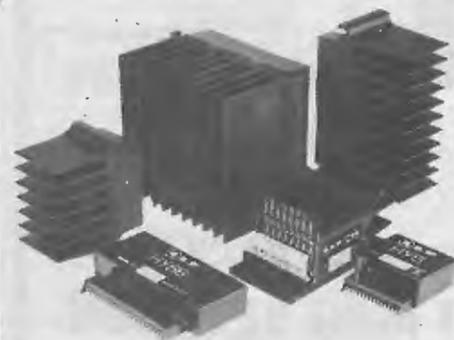
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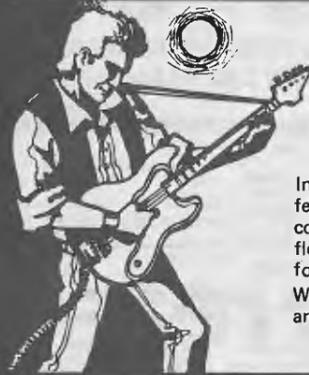
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Module Number	Output Power Watts rms	Load Impedance $\Omega$	T.H.D. Typ at 1KHz	I.M.D. 60Hz/7KHz 4:1	Supply Voltage Typ	Size mm	WT gms	Price inc. VAT
HY30	15	4-8	0.015%	<0.006%	$\pm 18$	76 x 68 x 40	240	£8.40
HY61	30	4-8	0.015%	<0.006%	$\pm 25$	76 x 68 x 40	240	£9.55
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HY124	60	4	0.01%	<0.006%	$\pm 26$	120 x 78 x 40	410	£20.75
HY128	60	4	0.01%	<0.006%	$\pm 35$	120 x 78 x 40	410	£20.75
HY244	120	4	0.01%	<0.006%	$\pm 35$	120 x 78 x 50	520	£25.47
HY248	120	8	0.01%	<0.006%	$\pm 50$	120 x 78 x 50	520	£25.47
HY364	180	4	0.01%	<0.006%	$\pm 45$	120 x 78 x 100	1030	£38.41
HY368	180	8	0.01%	<0.006%	$\pm 60$	120 x 78 x 100	1030	£38.41

Protection: Full load line. Slew Rate: 15V/ $\mu$ s. Rise time: 3 $\mu$ s. S/N ratio: 100db. Frequency response (-3dB) 15Hz - 50KHz. Input sensitivity: 500mV rms. Input Impedance: 100K $\Omega$ . Damping factor: 100Hz >400.

### PRE-AMP SYSTEMS

Module Number	Module	Functions	Current Required	Price inc. VAT
HY6	Mono pre amp	Mic/Mag. Cartridge/Tuner/Tape/Aux + Vol/Bass/Treble	10mA	£7.60
HY66	Stereo pre amp	Mic/Mag. Cartridge/Tuner/Tape/Aux + Vol/Bass/Treble/Balance	20mA	£14.32
HY73	Guitar pre amp	Two Guitar (Bass Lead) and Mic + separate Volume Bass Treble + Mix	20mA	£15.36
HY78	Stereo pre amp	As HY66 less tone controls	20mA	£14.20

Most pre-amp modules can be driven by the PSU driving the main power amp. A separate PSU 30 is available purely for pre-amp modules if required for £5.47 (inc. VAT). Pre-amp and mixing modules in 18 different variations. Please send for details.

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Model Number	For Use With	Price inc. VAT	Model Number	For Use With	Price inc. VAT	Model Number	For Use With	Price inc. VAT
PSU 21X	1 or 2 HY30	£11.93	PSU 52X	2 x HY124	£17.07	PSU 72X	2 x HY248	£22.54
PSU 41X	1 or 2 HY60, 1 x HY6060, 1 x HY124	£13.83	PSU 53X	2 x MOS128	£17.86	PSU 73X	1 x HY364	£22.54
PSU 42X	1 x HY128	£15.90	PSU 54X	1 x HY248	£17.86	PSU 74X	1 x HY368	£24.20
PSU 43X	1 x MOS128	£16.70	PSU 55X	1 x MOS248	£19.52	PSU 75X	2 x MOS248, 1 x MOS368	£24.20
PSU 51X	2 x HY128, 1 x HY244	£17.07	PSU 71X	2 x HY244	£21.75			

Please note: X in part no. indicates primary voltage. Please insert '0' in place of X for 110V, '1' in place of X for 220V (Europe), and '2' in place of X for 240V (U.K.). All units except UC1 incorporate our own toroidal transformers.

### MOSFET MODULES

Module Number	Output Power Watts rms	Load Impedance $\Omega$	T.H.D. Typ at 1KHz	I.M.D. 60Hz/7KHz 4:1	Supply Voltage Typ	Size mm	WT gms	Price inc. VAT
MOS 128	60	4-8	<0.005%	<0.006%	$\pm 45$	120 x 78 x 40	420	£30.41
MOS 248	120	4-8	<0.005%	<0.006%	$\pm 55$	120 x 78 x 80	850	£39.86
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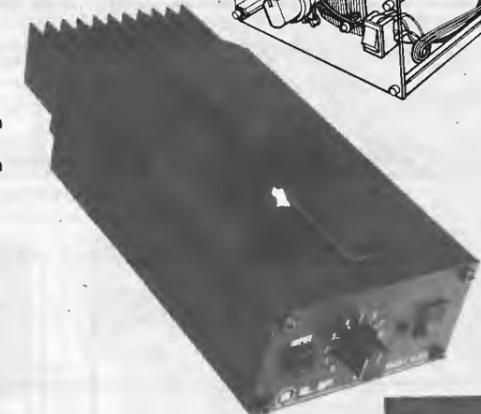
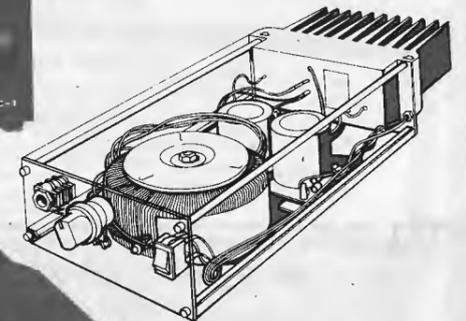
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UP6X	60W/4-8 $\Omega$	MOS	Mono	HiFi	£64.95
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US3X	60W/4-8 $\Omega$	MOS	Power	Slave	£69.95
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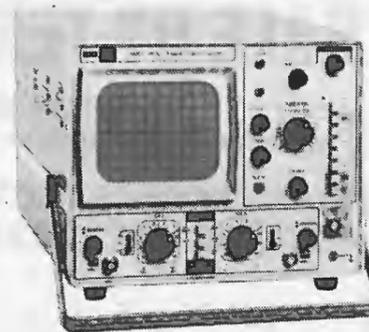
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## Impossible loyalties

A common assertion by those who have a vested interest in the retention by a company of engineering knowledge and skills is that engineers owe allegiance to the organization that employs them. Engineers, it is said, should preserve company secrets, even when it would be to the public good to disclose them, and should not behave in any way which would damage the organization, though it may be acting in an impossible manner.

Engineers, in short, must be loyal to their organization.

This is a curious use of the word 'loyal'. Two prerequisites must be present in a relationship before loyalty can enter – the two parties concerned must be people and the loyalty must work both ways – neither of which conditions can apply between an employee and his organization.

Loyalty is normally regarded as existing between friends or among people who work together. It may be possible to display loyalty to a football team or to a school or any other group, but it is to the people in the groups that the loyalty is shown. An organization consists of people, but in the sense in which employees are exhorted to be loyal, it is the organization itself which claims the loyalty. In such a relationship, there is no personal link to stimulate loyalty, which is a moral attitude, impossible to attribute to an organization.

Loyalty to an organization is rendered more meaningless by the lack of any return in the attitude. An organization does whatever it must do in its own best interests, heedless of any benefits or harm to anyone. It is completely impersonal and cannot display loyalty to any person. The link between organization and employee is therefore one-way only and loyalty cannot exist.

Loyalty is considered to be a praiseworthy attitude, and it makes little sense to describe as loyal a person who acts in a less than praiseworthy manner to demonstrate his loyalty. Could one be loyal to a mass murderer, or to a group of terrorists? How, then, could an employee be loyal, even if one is to disregard all the foregoing, to an organization which makes profits from the sale of offensive weapons, or seeks to work in any way against the common good?

It is in this area, of the direction of responsibility, that engineering professionalism needs a close look. A professional considers the interests of his client (employer) before those of the rest of society, regarding, in the process, the results of his work as being the responsibility of his employer.

This is an anti-social attitude of mind, which in the perilous 1980s should be closely re-examined, particularly when the professionals concerned are engineers.

# Data decoder for UOSAT

This high-performance correlation demodulator can decode data or picture information from the UOSAT spacecraft either directly off-air or from tape-recordings. It may be connected to a printer, v.d.u. or computer as the user wishes.

Since UOSAT's digital data is sent as 1200Hz or 2400Hz tones, a possible method of decoding it is to time the zero-crossings of the signal. Decoders based on this principle, however, are highly susceptible to noise and interference. Their performance depends on the audible signal-to-noise ratio, which is in turn directly dependent on the audio bandwidth; and the bandwidth cannot be reduced indefinitely without also attenuating the signal.

A more promising approach is to use a correlation decoder: this matches the incoming signal against synthesised replicas and in doing so extracts information much more effectively. In consequence its error performance is dependent only on the energy-density of the noise, which is independent of the audio bandwidth. In this way a signal can be decoded uncorrupted even though it seems to be buried in noise: for example, 45 baud data signals can be decoded without errors at a noise-to-signal ratio as poor as 5:1. This type of system is known as a matched filter.

The decoder described in this article comprises a channel filter, a 1200 baud demodulator, a 300 baud demodulator, a lock detector and a line-synchronization detector for the image data from UOSAT's c.c.d. television camera. Of these, the 1200 baud demodulator is central to the design; the other circuits may be omitted if the user does not require them. Alternative data-rates can be effected by changing timing components. The system does not include image display circuits since a design for these is available from AMSAT-UK<sup>1</sup>.

## Decoder outline

The decoder's task is to distinguish in the presence of noise between the two tones possible within a bit-period. The essential tool for this job is a correlator (Fig. 3). The signal to be detected is multiplied by its replica and the product is accumulated over a signal interval. Maximum output indicates a perfect match, zero output no match. Now, since 0 and 1 signals are mutually exclusive, the output of two such correlators may be compared to find the better match at the end of each bit-interval (Fig. 4). This is the matched filter. For timing, a bit rate clock is required, and must be extracted from the incoming sig-

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nal; this rate may be either 1200 or 300 baud. The video line-sync code may best be detected using a window correlator. As the name suggests, this inspects a short sequence of the data-stream as it passes by, looking for a particular pattern. In the case of the line-sync code, the window would

## Data transmissions from UOSAT

The satellite can transmit a variety of data formats at a number of popular speeds, as directed by ground-station command. The data includes telemetry, news bulletins and camera images.

Telemetry information is sent in 12-bit ASCII code: one start-bit, seven data, one even-parity and three stop-bits. A sample block is reproduced in Fig. 1. The first two lines are the 45 spacecraft status bits; the next six lines display 60 telemetry values, prefixed with identifiers 00-59. Translation of the three information digits is simple. For example, the right hand column gives temperatures of the six faces of the spacecraft, which convert as  $T = 0.2 \times (474 - N)$  degrees Celsius. A complete list is available through AMSAT-UK<sup>1</sup>. There are occasional variations to this format; explanations then accompany the data. The data rate is usually 1200 or 300 baud, although 45.45 baud (Baudot code), Morse code and 'Digitalker' synthetic speech are sometimes used.

News bulletins are sent as text and typically contain operational information, orbital data and acknowledgements of reception reports. The format is 11-bit ASCII with two stop-bits.

Image transmissions from the spacecraft's c.c.d. camera experiment have a 256x256 pixel format with a 16-level grey-scale (four bits). The ground area seen in an image is about 500km square<sup>2</sup>.

The transmitted sequence is illustrated in Fig. 1b, and is sent in a line-synchronous manner, i.e. 256x4 bits for each line, and 256 lines. Each line is preceded by a frame header. The line-sync code is 32 bits,

01011011101001000101101110100100

be 32 bits long with the correlator threshold set perhaps slightly below 32 'votes', giving some immunity from occasional corrupted bits.

## Processing

Since the signal carries virtually no information in its amplitude, hard-limiting it will allow subsequent multiplications to be carried out by exclusive-or gates (Fig. 5). The two accumulators and the decision-tester described above are reconfigured

(hex 5BA45BA4). Thus a line is 1056 bits long. The frame header consists of a shortened line composed of 31 line-sync codes, preceded by normal line-sync, and is 1024 bits long.

Pixels are coded 0000=black, 1111=white. MSB is sent first. A complete frame comprises 271360 bits, and at 1200 baud is transmitted in about 3.77 minutes.

Fig. 1a. Typical telemetry block from UOSAT. The two identical lines of status bits are followed by 60 telemetry values. These values may easily be decoded using the published calibration equations.

```
AMSAT 10100 10000 00000 00000 00100 00000 10101 11100 00000
AMSAT 10100 10000 00000 00000 00100 00000 10101 11100 00000
00440 01060 02690 03000 04000 05559 06750 07555 08447 09447
10140 11200 12000 13000 14027 15409 16822 17293 18448 19444
20170 21070 22672 23005 24007 25418 26422 27294 28494 29445
30330 31210 32665 33204 34013 35301 36374 37407 38510 39442
40140 41550 42699 43173 44041 45000 46003 47463 48486 49541
50180 51070 52283 53428 54609 55441 56015 57430 58507 59427
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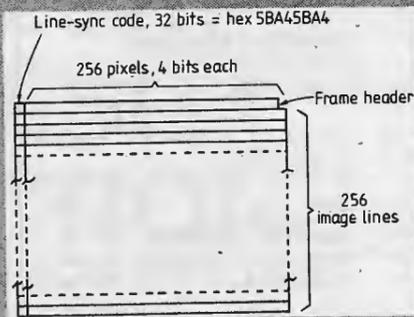


Fig. 1b. Data format of UOSAT's c.c.d. image transmissions. The frame header is a shortened line comprising 31 line-sync codes plus the normal line-sync code and is 1024 bits long. Each of the 256 image lines is 1056 bits long in total.

## Binary two-tone encoding

Data at 1200 bits per second is encoded as synchronous audio frequency-shift keying (a.f.s.k.) with one cycle of 1200Hz for 'mark' and two cycles of 2400Hz for 'space' (Fig. 2). This audio then frequency modulates the RF carrier, and may be detected using an ordinary amateur n.b.f.m. receiver, preferably with the de-emphasis reduced to about 50 microseconds so as to preserve correct phase relationships. Other baud rates use the same coherent tones, but bit transitions occur asynchronously; the modulation is inverted with respect to that used for 1200 baud.

Note that the ASCII polarities are: space=start=data 0, and mark=stop=data 1. For the c.c.d. image, 0=1200Hz and 1=2400Hz. The f.m. deviation is quite small: at 145MHz it is 600 and

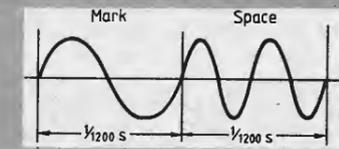


Fig. 2. Synchronous two-tone a.f.s.k. encoding. At 1200 baud, as shown here, data is synchronous. At other speeds, data is asynchronous and transitions occur at random phase angles within the tones. These audio-frequency tones modulate UOSAT's carrier on 145.825MHz or 435.025MHz.

1200Hz for the two tones, although at 435MHz it is somewhat wider. The maximum doppler shift for the 145MHz transmission is  $\pm 3.5$ kHz, with a rate-of-change reaching 50Hz/s on an overhead pass.

here as a subtractor followed by a single accumulator. At the end of each bit-interval the decision is clocked into an output buffer and the integrator's output is zeroed in readiness for the next bit.

To generate the tone replicas (which may now be square waves) and to provide timing signals, a 1200Hz clock is extracted from the input signal using a phase-locked loop (p.l.l.). This acts on both tones, the contribution from the 2400 product being weighted half that of the 1200 product. A loop-gain of 1500 ensures that static phase errors are kept to a minimum; these might otherwise be troublesome because of oscillator drift or because of speed variations when decoding data recorded on tape. This gain corresponds to a voltage-controlled oscillator swing of 750Hz with respect to a nominal frequency of 1200Hz. With off-air signals the loop-bandwidth can be as little as 2Hz before acquisition of lock becomes inconveniently slow. However, during tape replay the bandwidth must be narrow enough to minimise the effects of signal noise though wide enough to accommodate speed variations in the tape machine, especially wow. With a cheap cassette machine the figure is likely to be about 20Hz.

A p.l.l. is merely a continuous correlator with feedback arranged to drive the phase of its replica to yield an average correlation of zero. This condition also occurs when the input is random noise; so it is useful to include a lock-detector. Lock can be indicated by a meter.

In synchronous 1200 baud mode, the bit-rate clock is by definition provided by the signal tones; however, at asynchronous rates (e.g. 300 baud) the clock must be extracted from the data itself. The data must therefore be detected first in some non-synchronous way, and for this a simple RC filter is sufficient (Fig. 6). The spectrum of this random data signal has a null at the bit-rate, but it does have energy at half the bit-rate. Thus if the data is squared, a spectral component will appear at the bit-rate with constant phase, which is what is required. A suitable way of doing this is to exclusive-or the data with itself delayed by half a bit-period. This generates a single cycle of bit clock for each data transition. This signal can be made contin-

uous by another p.l.l., which can then be used to operate the data-correlator's dump-reset and so provide coherent detection.

Image line sync detection is effected by clocking the detected 1200 baud data into a 32-bit shift register (Fig. 7). The output from each stage is added or subtracted in an analogue summing circuit, according to whether the bit to be tested is a 1 or a 0. When all 32 bits are nesting in the 'memory' maximum output is obtained from the summation. A clipping threshold set at, say, 30 'votes' allows for up to two

bit errors. It should be noted that since the line-sync code contains 16 bits repeated, there will be a half-amplitude correlation peak 16 time slots before and after the main peak. This is caused by the first block of code (hex 5BA4) passing through and matching the template provided for the second block, and vice-versa. If this peak were not present then the voting threshold could be set even lower. The code is not ideal.

## Circuit notes

The complete circuit diagram is shown in Fig. 11. Although the system was designed for 12V operation, it will work with supplies between 6V and 18V. (For supplies above 15V, cmos devices numbered with a 'B' suffix should be used.) A half- $V_{DD}$  bias is incorporated to 'float' the op-amps. Wire-wrap construction was used for the prototype, with components mounted on dil headers for easy experimentation. Layout is not particularly critical, though it would be prudent to keep the input circuits and the two p.l.l.s apart to minimise stray pick-up.

The channel filter has a 3dB cut-off at 3000Hz and is a fifth-order Bessel type, with a very flat group delay (about 135 microseconds) which introduces no ringing or phase-distortion. Interstage a.c. coupling reduces the response below 300Hz. Equivalent noise bandwidth is

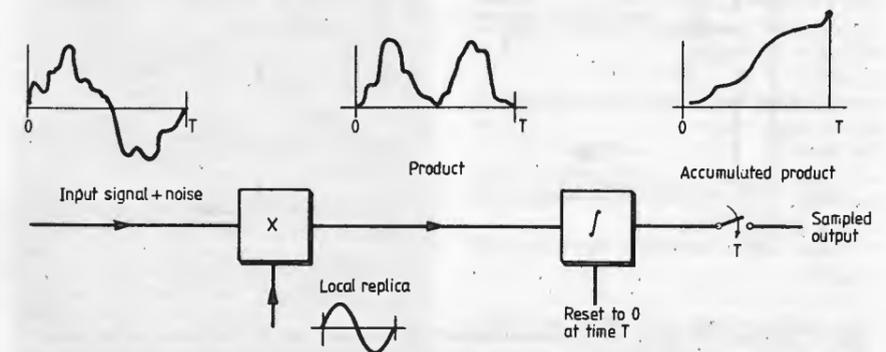


Fig. 3. Basic elements of a correlator. A (noisy) incoming signal is multiplied by a perfect local replica and the product is integrated. At the end of the data interval the resulting accumulation is tested. The accumulator is then usually reset and the process repeated. If the signal exactly matches the replica, the output is at a maximum.

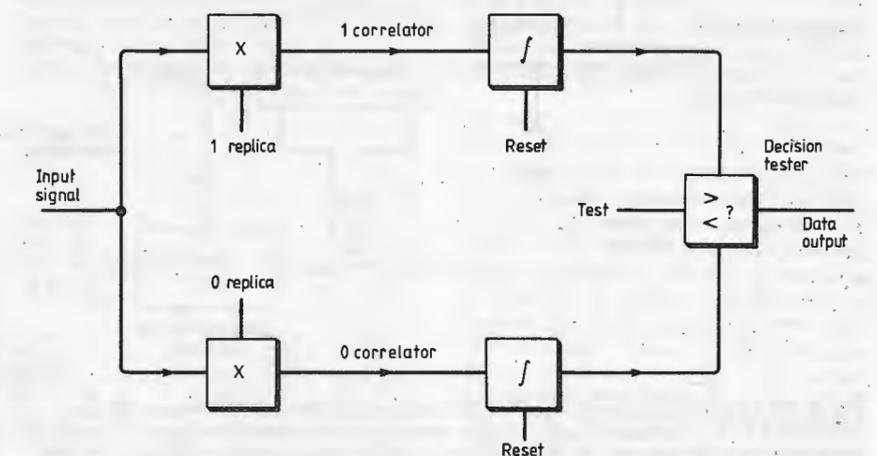


Fig. 4. A matched filter. The output of a pair of correlators is tested to find the better of the two matches. In the practical circuit, this decision is effected by a subtraction operation.

3300Hz. The filter is not essential when using de-emphasised signals from a typical f.m. receiver. However it must be used if wide-band noise is present during, for example, performance testing or with signals direct from the receiver's f.m. discriminator.

The limiter (IC<sub>1c</sub>) will operate on a few millivolts of signal. The input polarity-invert switch S<sub>2</sub> is needed as receivers and tape-recorders will have arbitrary inversions built in, and the polarity of 1200 and 300 baud signals differs. The signal presented to the multipliers must be in the correct sense.

The main p.l.l. (IC<sub>2</sub>, IC<sub>3</sub>) operates at 19 200Hz. It is followed by a four-bit divider and some logic to generate the replicas I:1200, I:2400, Q:1200 and Q:2400 together with the synchronous integrate-and-dump timing. The circuit has a loop bandwidth of 20Hz.

An inspection of the waveforms entering the integrator (Fig. 8) shows that accumulation occurs only during the second and third quarters of the basic 1200Hz rhythm. (Because the tones have lost their sinusoi-

dal character through limiting, it is only during this period that they differ.) Thus in synchronous 1200 baud operation the decision 'transfer to output buffer' can take place at the 3T/4 point, and the capacitor can be reset at leisure during the succeeding fourth and first periods. During asynchronous operation, however, 'dump-and-reset' can occur at random times and must be accomplished rapidly.

Acquisition of lock in the main p.l.l. is detected by summing the product of the signal with I:1200 and I:2400. Lock information is available during the first and fourth quarters; the analogue switch IC<sub>7c</sub> admits only this energy to the op-amp RC smoother IC<sub>8b</sub>. The circuit has a gain of 10 to emphasise marginal lock conditions and will 'end-stop' otherwise. A bistable output buffer (IC<sub>9b</sub>) is used as, being on the same chip as the data output buffer, it will have the same threshold.

Extraction of non-coherent data is effected by the continuous correlator R<sub>23</sub>, R<sub>24</sub>, C<sub>14</sub>. The time-constant or 'memory' should be short enough to avoid excessive inter-bit interference but long enough to



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smooth out noise. A value of a quarter to a half of a bit period is usual. The time-constant used introduces a quarter-bit lag, which is convenient for subsequent timing requirements. The asynchronous data may be used directly from this point if required, though its timing will be very ragged and the error rate somewhat high. The analogue switch IC<sub>7b</sub> is only 'on' during the second and third quarters of each 1/1200s period: this keeps out non-information during the first and fourth quarters and at the same time prevents decay of the capacitor voltage and hence loss of information already stored.

To extract the asynchronous bit clock from the 300 baud stream, an eight-bit shift register IC<sub>10</sub> is clocked at sixteen times the bit rate to provide a half-bit delay. The first and last stages are exclusive-or gated to generate a noisy bit clock which then feeds the second p.l.l., IC<sub>11</sub> and IC<sub>12</sub> (another correlator). A four-bit divider and logic provide the bit clock replica I:300 and the carry is used to reset the data correlator as described above. Circuit values shown are for 300 baud; other rates require the values of C<sub>12</sub>, C<sub>14</sub>, C<sub>15</sub>, C<sub>16</sub> to be changed pro rata. The p.l.l. bandwidth is about 1Hz. A lock indication is obtained by multiplying the noisy bit clock by Q:300 and smoothing the result.

The c.c.d. line-sync detector is a 32-bit shift register and consists of IC<sub>9a</sub> for the first bit and IC<sub>14</sub>-IC<sub>17</sub> for the remaining 31. On the circuit diagram, bits are shifted from right to left.

No output buffering is shown in the diagram: the user should add it as required. At the output, ASCII start-bit polarity and data 0 are high, stop and data

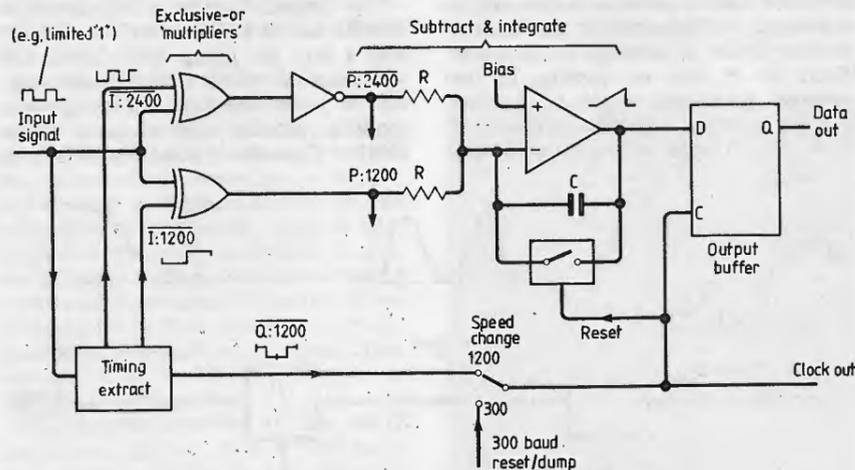


Fig. 5. Outline of the decoder. A phase-locked loop extracts the 1200Hz clock signal and generates the replica signals. The input signal is 'multiplied' by the replica signals in the exclusive-or gates; the op-amp compares the result by subtraction and integrates it.

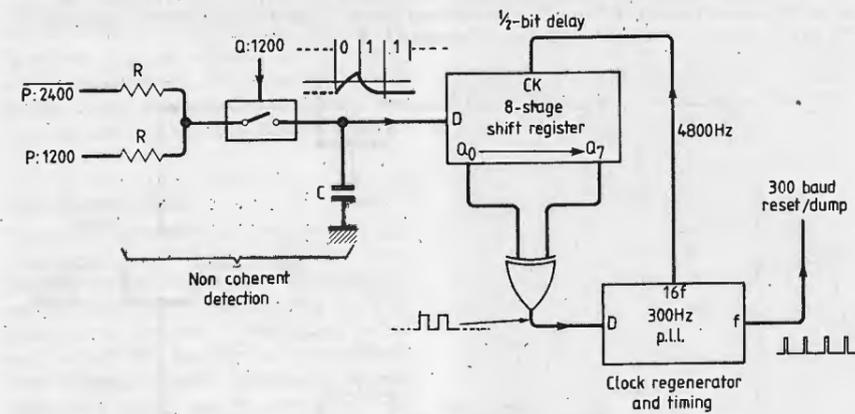


Fig. 6. 300 baud bit-clock extraction. The 300 baud signals are asynchronous and data transitions do not necessarily occur at zero-crossings of the transmitted tones. The data is multiplied by itself delayed, to give one cycle of 300Hz for each data transition. A narrow-bandwidth p.l.l. regenerates from this a steady 300Hz bit-clock which is used to drive the reset-dump section of the coherent detector in Fig. 5. Note that the non-coherent detector effectively is the same as the integrator of Fig. 5, with R replacing the reset switch.

1 are low; image bits from the c.c.d. camera are 1 high and 0 low; data clock is significant on high-to-low transitions; lock and line-sync are high true and are synchronous with data output.

### Setting up

An accurate audio generator, oscilloscope and multi-meter will be needed, as well as a telemetry test data tape. To set up the line-sync detector it is necessary to have a c.c.d. data tape. These signal sources may be either recorded off-air or obtained via AMSAT-UK. (The data on the latter's tapes differs slightly from the format now transmitted by UOSAT. However, this does not affect their use.)

**Main p.l.l.:** apply noise to the signal input (noise from the receiver will do). Using R<sub>66</sub>, adjust the v.c.o. of IC<sub>2</sub> to 19200Hz. If this cannot be effected change the timing capacitor C<sub>10</sub>. Do not change resistors, as this will affect the p.l.l. performance characteristics. A 4:1 spread in nominal oscillation frequency of a 4046 chip is quite typical. Applying 0V and then V<sub>DD</sub> to pin 9 of the p.l.l. chip IC<sub>2</sub> should result in a total frequency swing at the divide-by-16 output (IC<sub>3</sub> pin 15) of about 700Hz.

**300 baud p.l.l.:** adjust the centre frequency to 4800Hz with R<sub>67</sub>; if necessary alter C<sub>16</sub> to achieve this. Total frequency swing should be 600Hz at the divider output (IC<sub>12</sub> pin 15).

**Half supply voltage:** still with noise applied to the input, switch to 1200 baud operation and adjust the half-supply-voltage control R<sub>65</sub> until the output buffer bistable yields 1 and 0 with equal frequency. This may be easily observed by connecting an analogue voltmeter between the Q and Q outputs of IC<sub>9a</sub>, pins 1 and 2. It should read zero.

**Performance checks:** apply a 2400Hz tone to the input and verify that the main p.l.l. locks and continuous 1 data is output. Repeat for 1200Hz and observe continuous 0 data. Flip the input invert switch. There

Fig. 7. Line-synchronisation detector for UOSAT's c.c.d. image transmissions. A 32-bit window-correlator offers excellent immunity from corrupted code bits. When the code to be detected (hexadecimal 5BA45BA4) arrives in the shift-register, the output of the analogue summer reaches a maximum. If the threshold is set at, say, 30 votes out of the possible 32, errors in up to two bits will be tolerated.

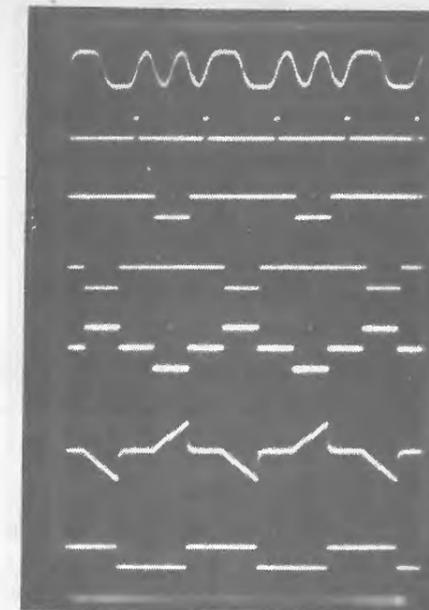
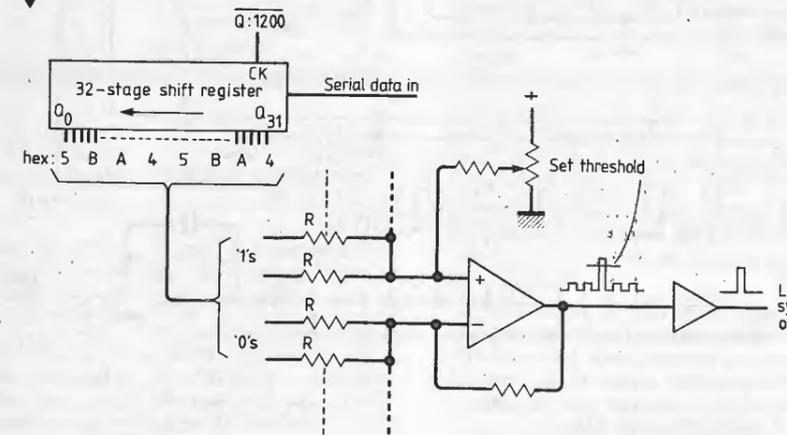


Fig. 8. 1200 baud waveforms. Traces a to g show 5-bit noise-free signals from a test source. The horizontal scale is 417μs per division. When noise is present, the triangles in trace f become ragged and diminished.

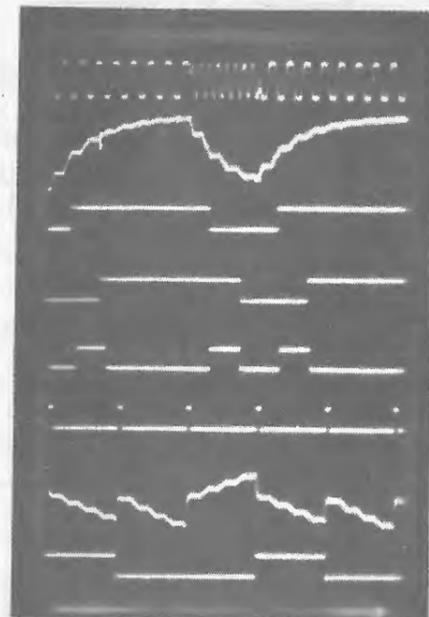


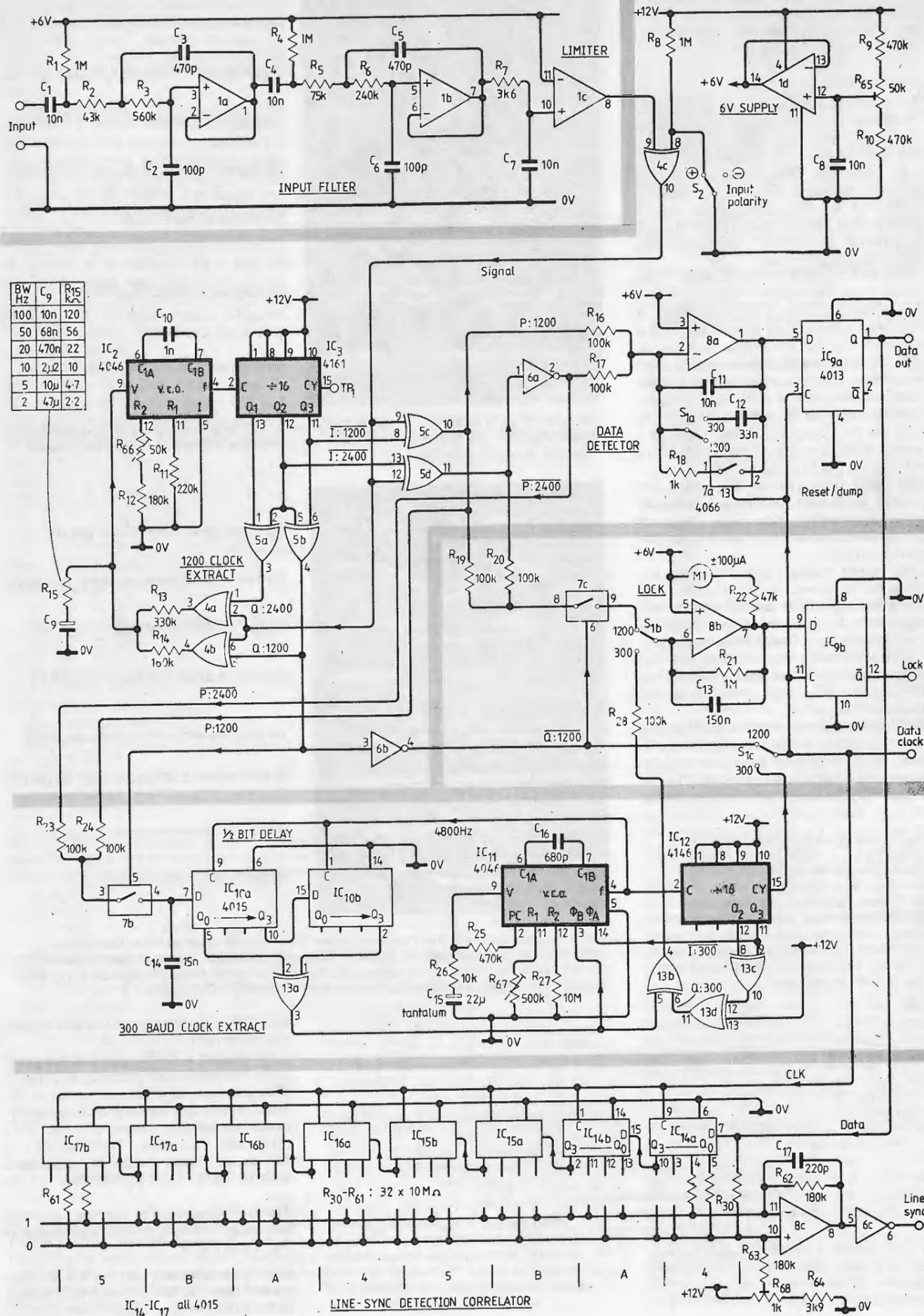
Fig. 9. 300 baud waveforms. Horizontal scale is 1.67ms per division. Note that signal transitions of the input data are asynchronous with respect to the tones. Each transition in trace b gives rise to one proto-cycle of 300 baud clock, which is regenerated by a p.l.l. as in trace f. The total data-processing delay is equivalent to one bit-period.

should be a momentary loss of lock-indication while the p.l.l. recovers.

Now inject a 150Hz signal at the input to the 300 baud clock extractor IC<sub>10</sub> pin 7. This simulates 101010.... reversals at 300 baud. Verify that the loop locks properly. Check for similar operation using 75Hz (11001100....), 50Hz (11100011100....), and so on. Lock should be maintained with 18.75Hz (1111111100000000....) input.

The system can now be checked out using test tapes, referring to the waveforms in Fig. 8 and Fig. 9.

**Line-sync detector:** play the c.c.d. camera test tape into the system, which should be set to 1200 baud. Observe the bit sync

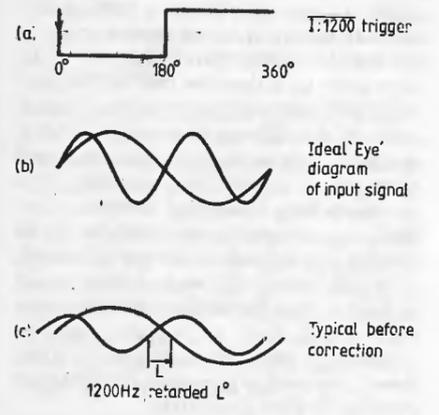


**Fig. 11.** The complete data demodulator. 1200 baud or 300 baud decoding is selected by S<sub>1</sub>. Op-amps are TL084 or equivalent, exclusive-or gates are all 4070 and inverters 4069. C<sub>2</sub>, C<sub>3</sub>, C<sub>5</sub>-C<sub>7</sub>, C<sub>10</sub>, and C<sub>16</sub> are polystyrene, 5% tolerance.

correlator output IC<sub>8</sub> pin 8. At the end of each line the 'peak' will be clearly visible, as will minor peaks. Now add noise to the input signal, sufficient to start creating data errors. The peak will be seen occasionally to drop by one or two votes as the noise is increased.

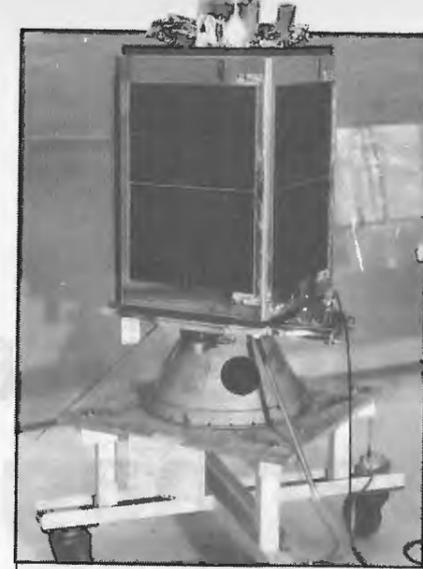
Adjust the threshold control R<sub>68</sub> so that the peak just crosses the output buffer threshold on 32, 31 and 30 votes, but not on 29. (This is easier to do than describe!) There is little point in going lower: at a bit-error rate of 1 in 12 the image would be useless yet there would still be an even chance of sync detection.

**Main p.l.l. loop bandwidth:** the aim in selecting the loop bandwidth is to minimise the combined effect of noise and tape-recorder wow. To achieve this, record about ten minutes of 2400Hz sinewave tone on the recorder. An initial loop bandwidth of 20Hz should be used. Replay the tape and, triggering off the p.l.l. output, estimate the peak-to-peak timing jitter T<sub>j</sub> seen on the input signal. Now input the 2400Hz tone directly from the audio oscillator. Gradually add noise until the data output at 1200 baud begins to give spurious zeros at a rate of about one per second. Measure the peak to peak jitter once again, T<sub>n</sub>. The optimum bandwidth is roughly equal to 20 × T<sub>j</sub>/T<sub>n</sub>. Use the



Angle L/45°	CR μs
0.1	1260
0.2	622
0.3	404
0.4	293
0.5	223
0.6	173
0.7	134
0.8	102
0.9	70

**Fig. 10.** At the input, the 1200Hz tone will probably be retarded with respect to the 2400Hz tone. A suitable CR phase-compensation network can be selected from the table. If instead the 1200Hz tone is found to be advanced, R and C should be interchanged to give a low-pass network. The left-hand column of the table would then have to be re-labelled "1-L/45°".



The amateur scientific satellite UOSAT, built at the University of Surrey, was launched by NASA on 6 October 1981. Its 515km-high polar orbit has a period of approximately 95 minutes. UOSAT's two main data beacons transmit on 145.825MHz and 435.025MHz; reception is possible during favourable passes on an ordinary amateur two-metre receiver with a quarter-wave whip aerial. A recorded news bulletin which also gives orbital predictions is available by telephone on Guildford (0483) 61202.

table to select new components for R<sub>15</sub> and C<sub>9</sub>. Replay the tape; peak to peak jitter should be less than about 40μs. If it is significantly larger, then the performance will be degraded.

**Phase problems**

A correlation decoder is only as good as the assumptions implicit in its design. Most fundamentally, the input signal (limited) and the replicas should be identical. During the passage through the transmitter, receiver i.f., f.m. discriminator, de-emphasis, audio amplifier and possibly a tape recorder some relative phase shift of the 1200 and 2400Hz tones is inevitable. Full performance will only be realised if this is corrected.

To examine this, trigger the oscilloscope from the main p.l.l. 1:1200 signal, one sweep per bit, and examine the input signal where 0 and 1 tones will be seen superimposed. The ideal is depicted (noiseless) in Fig. 10b; note the equal amplitudes and the crossover exactly in the middle.

Most likely it will be found that the 1200Hz tone is of larger amplitude, and slightly retarded (Fig. 10c). This can usually be cured with a CR high pass network at the system input (Fig. 10d). Adjust components until the crossover sits on the zero line as in Fig. 10b. If the 1200Hz tone is advanced than an RC low-pass network should be used.

Any problems (such as ringing) should be investigated and the source located. It may be found advantageous to bypass the receiver's audio stages. Signals could also be taken directly from the f.m. discriminator and separately de-emphasised.

**Performance**

If we define 'negligible errors' as an error rate of 1 in 10<sup>5</sup>, for a data rate of 1200 bit/s and bandwidth 3300Hz the 'audible' signal to noise ratio should exceed 7.3:1, a signal at the receiver r.f. input of about 0.2 μV into 50Ω. So far as it is possible to measure this with precision, the figure is borne out in practice.

Excessive noise such as vehicle ignition spikes are a nuisance on weak 1200 baud signals; since they are typically of 1ms duration they can obliterate a whole bit. No add-on decoder can cope with this situation - it is a receiver problem, created in the f.m. de-emphasis network, which stretches noise that in the i.f. bandwidth once had a harmless duration of a few tens of microseconds. The problem is much reduced by taking signals direct from the discriminator.

At 300 baud the expected 6dB noise performance improvement over 1200 baud operation is realised (though at a quarter of the information rate). The decoder is virtually immune to ignition spikes, since a 1ms pulse will only squash about one-third of a bit, leaving the other two-thirds unaffected (albeit 2dB more vulnerable to other noises). The bit sync extractor will work quite satisfactorily on signals of only one bit in eight, at signal-to-noise ratios too small to be useful.

It should be remarked that the decoded data can be further processed by computer before display by a v.d.u. or printer. 12-bit ASCII (for example) contains five or six redundant bits, yet an error in any of these will cause a misprint of the true character. In fact, of the 6336 bits in a telemetry frame only 765 are information-bearing. Post-detection processing could obviate the effect of errors in the other 5571 bits.

For displaying the image data on a television screen, a converter design is available from AMSAT-UK; printed circuit boards will be offered when the commissioning of the c.c.d. camera has been completed.

**References**

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# The doctrines of Copenhagen

*The doctrines (literally, teachings) of the Copenhagen School served to detach the modern quantum theory from common sense. The key to the aberration was the diehard refusal to admit that the traditional field-theory concept of continuity, on which the wave theories are based, is incompatible with discrete and discontinuous quanta, or particles.*

I have called much evidence in the *cause célèbre* of Physical Realism versus the Copenhagen School, but the evidence I have called is only a very small fraction of the physical evidence available. I have called no mathematical evidence at all, and indeed I have been careful to avoid mathematical argument of any kind. It is true, as Galileo said, that mathematics is the language of physics, but as far as I am concerned that is as far as it goes. It is not a particularly good language from a physicist's point of view and sometimes, as for instance when it is asked to handle simple matters like Fresnel diffraction or the length of the circumference of a planet's orbit, it can prove distinctly awkward and inelegant. Certainly Sir James Jeans was over-enthusiastic when he created God in his own image by claiming Him to have been a mathematician, but his attitude was perhaps not extreme for the 1930s era when most of the dubious doctrines were propounded. A prime difference between physics and mathematics is that physics is, or should be, subject to the strict discipline of the experimental method, whereas mathematics is not. The case that I must now summarize on behalf of the prosecution is a case in physics, not mathematics.

I believe there can be little doubt but that modern physics took a wrong turning in the 1930s. The outward and visible sign of the trouble was a denial of realism in natural philosophy and the espousal of a particular mysticism in its place. As far as I have been able to discern it was the result of a purely human whim, odd perhaps but understandable in that post-war period; for none of the reasons commonly advanced as causes of the philosophical revolution can stand up to a cold, scientific inquisition either together or severally. We can be reasonably sure, at any rate, that the real causes were not technical — it would therefore seem unprofitable to

hazard guesses as to *why* it all happened, which is a question more for a psychologist or comparative theologian than for a physicist. Closer to home we can examine *what* went wrong and how it went wrong, as steps from which we may obtain hints toward our aim of eventual counter-revolution — that is, of trying to put modern physics back onto the intellectually honest philosophical road.

I have said enough about the three really glaring philosophical crimes of the Copenhagen School, their confusions of matter-waves with probability theory, of meta-

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physics with physics, and of measurement with fact, not to have to rediscuss them here. They were outstanding. However, there has always been a tendency to allocate to physical theories an importance of a more fundamental kind than they really warrant. One instance of this is the doctrinaire concept of the physical reality of the electromagnetic field. If we take note of what experiment actually says, as opposed to what we might prefer it to say, we find that light *in vacuo* is not influenced by electric or magnetic forces, and we may deduce from this that neither light waves nor photons can be of electromagnetic origin; it is *electrons* which are affected by such forces, not photons! The great Electromagnetic Theory appears as an analogy of Nature, sometimes as a very useful and accurate analogy, sometimes as a definite failure, but at no time does it seem to afford us a sound conceptual model of the working of the real, physical world.

Conceptual models are, in fact, of very great importance in physics. They enable one experience to be correlated with another so that the whole becomes greater than the sum of its parts and *scientific progress* is thereby made. Such models enable us to visualize the concepts within theories: the earth rotating, not the heavens; planetary electrons orbiting an atomic nucleus; the electron itself, a tiny torus of energy spinning mechanically at the speed of light. But during the 1930s there grew up a doctrine that the "master texts" of modern physics must lie in one or other of the differential equations of the quantum mechanics, and that one need never expect to be able to translate *those* equations into conceptual models — indeed, any attempt to do so tended to be derided as mechanistic and old-fashioned. (The real reason why such models cannot be built is that the mathematical concepts they would have to express, such as "symmetric and asymmetric wave functions", are neither physically plausible nor credible, in their application.)

In its most extreme form this doctrine of mathematical supremacy claims that the unprovable mathematics of the wave theory represents reality and that the physical world of our senses — and of our scientific instruments — is an illusion, a set of moving shadows on the wall of Plato's cave. Some people do actually believe this, but I assure you there is no experimental evidence of any kind to support it and it is the purest fancy. Its appeal is to the innate mysticism which haunts the depths of every human mind. In more practical form, but still fanciful, it becomes the doctrine of the New Mechanics, which says that the old-style mechanics of Newton and Galileo has been proved wrong and must be replaced by a new and correct mechanics, namely the "wave" or "quantum" mechanics. Two comments

may be offered in reply to that self-aggrandising claim. The first is that experiments in microphysics have *not* shown the older mechanics to be wrong, but merely to be incomplete — and correctably so. The second is that according to the proposed new mechanics the motion of the earth in its yearly journey around the sun is not controlled by a force of gravity (Newton) or by spacetime curvature (Einstein), but by a system of matter-waves of frequency "perhaps" —  $10^{66}$  cycles per second — yes, negative, going the opposite way! — which *maintains its coherence precisely all around the orbit*. You and I do not have to believe such far-fetched imaginings.

In a way it is to our advantage to have such an obvious example of failure of the wave theory in front of us, because it encourages us to go ahead and to question some of its other doctrines. I would like to spend a few moments now on the doctrine of the Observer. This arose, you may recall, in an attempt to evade the consequences *inter alia* of the infinite phase velocity of de Broglie or Schrodinger-type "matter-waves" by declaring them to be "unobservable". It was argued that a physicist should not ask questions about anything that he could not observe, and in due course the doctrine became enshrined as a Principle of modern physics: "No quantity which cannot be 'observed' is of any concern to science".

Now that statement has a fine, "fundamental" ring to it, but its true meaning was that the physicists of the Copenhagen School were preparing to shirk some of the duties of their profession. It leads straight to the following:

"An electron can be observed only when it interacts with matter or radiation: therefore it is of no concern to physics while it is in empty space".

The quotation is from Dirac, I believe; Bohr agreed with him. The argument was actually advanced to evade the problem of the indivisible electron in a "diffraction" experiment — ignore it and it may go away! A more conscientious view is that physics is the study of the workings of inanimate Nature, and that it should be concerned with *all physical phenomena whether we can observe them or not*. On this view the previous statement might read, with a more graceful humility:

"We infer that an electron in free translational motion obeys the conservation laws, although we accept that we cannot confirm experimentally that it does so". (In fact, of course, within certain limits we can.)

The real danger of this doctrine of the observer does not lie in its assertion of the irrelevance to physics of "unobservable" fundamentals such as, for example, the mechanical structure of an electron as a physical particle, although by categorising them as improper questions it has in practice inhibited discussion of them for fifty years. Much more serious philosophically is the assertion that since we cannot "observe" an electron (or any other particle) between its interactions with other particles or radiation, the electron *may go wherever it pleases* between such interactions. The argument runs that as we cannot observe it during the interval we

cannot prove that it obeys the conservation laws during the interval — or, more to the point, we cannot disprove the contrary, as in article 8 (page 62, April issue).

This has two very important illogical consequences. First, it renders the Copenhagen concepts of microphysics unimpeachable on internal grounds, because whenever these concepts call for violation of the conservation laws (as they frequently do) the defence has only to cry "unobservable" and the prosecution, however valid, must then collapse — *if* one accepts the magnificent, self-sustaining doctrine of the observer.

The second consequence is that the disciplines of physics and logic can now be bypassed with impunity: anybody henceforward can advance any "theory" without deference to physical discipline, except perhaps in the form of polite lip-service; for he has only to include one "unobservable" (or "virtual") quantity to ensure that his proposal cannot be disproved, either theoretically or experimentally. And if, like any other article of faith, it cannot be disproved, then one cannot in logic deny that it *might* be true. I am sure that my physicist colleagues will be able to call to mind at least half-a-dozen such pseudotheories in "modern physics" without assistance from me.

This variant of the observer doctrine is highly mystical, as it declares that a particle may pass from observed point A to observed point B without ever having to traverse the "unobservable" region in between. (The hard-headed layman will scarcely credit that this is the established doctrine of our modern physics, but I promise I'm telling the truth). The idea was first used publicly by Dirac in a mystical attempt to "explain" the positron (or positive electron), which did not require explanation anyway so much as acceptance. Dirac's proposal originated the "negative matter" concept which appears in some science fiction. (But if the mass of a positron were negative, as he was suggesting, then the energy released on "annihilation" would not be  $2mc^2$  but zero!). A less

startling application of the doctrine is found in the so-called tunnel effect, which is instructive enough to warrant an examination here. The story goes like this:

"Potential barriers", which prevent the free passage of electrons and other particles, seem to exist in a variety of situations in physics — surrounding the atomic nucleus, for example, or at a point of bad electrical contact between two conductors. A sheet of ordinary insulating material can be said to be a potential barrier in this sense. On the face of it no electron should be able to pass such a barrier unless it has enough energy — say several hundred electron-volts — to pass "over" it, as it were, by breaking down its insulation; yet experiments indicate that low-energy electrons, admittedly in very small numbers, do regularly appear at the far sides of such barriers. They must "tunnel" through them. How?

The wave theory waffles speciously about matter-waves which are in an "evanescent mode" while inside the barrier and which therefore (so conveniently!) are not *quite* like the waves of "real" particles; it does not explain how the electrons can appear at the far side of the barrier without having passed through it, but merely asserts that they do, "take it or leave it". We need not take it, because this is not just another Copenhagen *non-sequitur* but a simpler matter, more subtle and more significant. Consider the sand-fort built by children on the beach. Father fills it with sea-water for them from a bucket to within a few inches of its top. They paddle in it carefully for a while, without splashing. The energy of the water molecules is never sufficient to allow an appreciable number of them to pass over the barrier wall; yet half-an-hour later the outside of the wall is damp and the interior of the fort is empty. The principle is the same whether the process takes a microsecond or a thousand years.

The fallacy of the tunnel effect resides in the field-theory-type assumption that a potential barrier can properly be represented

*continued on page 65*

## A catalogue of error and failure

"Mathematics is the language of physics", but it is not subject to the discipline of verification by physical experiment and it can indulge its fancies *ad libitum* among the "unobservables". Realistic physics may not. Confusions of matter-waves with probability theory, of metaphysics with physics, and of measurement with fact, lie at the root of our serious problems today. Physical theories are not to be regarded as expressions of Revealed Truth but as analogies, sometimes useful and almost correct, sometimes so badly wrong as to be positively misleading. Conceptual models also are important in physics; an inability to support a credible conceptual model may be taken as an indication of the imminent failure of a theory. The doctrine of the Observer is particularly insidious because in fact, (if not explicitly) it removes from any new theory,

hypothesis or postulate the need to comply with physical discipline; a fine example of the kind of error which ensues is afforded by the conventional, artificial argument of the "tunnel effect". The most glaring of the philosophical errors of the Copenhagen School was concerned with self-justification and the "completeness" of its pet theory: it was claimed that because its own particular, illogical amalgam of matter-waves and statistics could not cope with individual microphysical particles, it was impossible that any other theory could. That was an excessive claim, for there are alternative possibilities of a less mystical and more realistic kind. If Copenhagen cannot deliver the goods, let us shop around for another paradigm that can. (See "The structure of scientific revolutions" by Thomas S. Kuhn, Chicago 1970.)

# IBM Selectric to TRS80 interface

This assembly language program, together with the inexpensive circuitry given in the April issue and a second-hand IBM Selectric typewriter, are all that is needed to produce a low-cost letter-quality printer

If you are not into assembly language programming then just skip this explanation, unless you want to learn a little about this powerful method of controlling your computer. I had to use assembly language because of the speed necessary in such a process as printing. Any other language would be out of the question. So let's jump right in.

Lines 100 to 330 as shown in the listing, which by the way is how the TRS editor/assembler assembles a machine-language program, give some useful information. If you use this program alone, you have to be sure that the line printer control block is initialized to point to this particular program. Locations 16422 and 16423 can point to anywhere in memory, and it usually points to the print routine in rom, but we definitely want it to point to where our program starts. So we have to initialize it to point to where we want. Lines 240 and 250 show what to poke where. If your own program is in a different part of memory, you'll have to change these two bytes. I have some other programs running at the same time as this one, such as a keyboard debounce routine. What I usually do is to have these other small programs initialize these locations for me when I first load them. It is simple to do and you don't have to remember to do it all the time.

Line 330 indicates that this program uses an ANSI typing element, or typeball. This element has the special symbols 'greater than' and 'less than' as well as the crossed zero. The parts list gives the number of this unit, and can be ordered from IBM for around \$20. If you use a standard element, the modified listing shows what lines have to be changed to get upper and lower case.

So now we can really get to the meat of the program. Line 360 tells the editor/assembler where the origin or beginning of this program is to be assembled from. If all the addresses that will be referred to in the program, such as absolute or relative jumps and subroutine addresses, are given symbolic names, then to assemble this program in a different location, the ORG is the only address that need be changed; a very handy feature. However, if you jump to a location in rom, you either have to give

the address specifically or define a special word for it; but that is part of the assembler's job and we won't go into that now.

The rom has already put the character to be printed into the C register, so in line 370 the first thing to do is to put it into the A register, or accumulator, so that it can be worked on. The next instruction clears the flag register in case any computations have to be made. In line 390 we check for the ASCII character for top of form. This character can allow us to get to the top of a

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form or page. It isn't used in our printing process, but is there just in case we need to use it some day. If it was that character, the program will jump to line 460. If not, we go to the next line, 410, which will check for a form-feed character. A form feed will allow line feeds to the end of a page. If it wasn't a form feed then the program will jump to line 530 which will output the character. Let's say it was a form feed, then in line 430 you see a fast way to zero the accumulator.

The line printer control block is initialized by rom. It normally puts the value 67 into the lines per page location at 16424.

This is alright for continuous paper, but not very useful for single sheets of typing paper. So instead we have either poked the value 54 here, or have had another assembly language program initialize this section. The rom has also placed the printer control block address into the IX register, so in line 440, IX+3, which is the lines/page value, is or-ed with the accumulator to be sure there is something there, if not, a null is printed. As there is something there, in line 460 this value is put into the accumulator and subtracted with the line counter, which has been incremented by one for each carriage return. The result is put into the B register. Next, in line 490, the character for a line feed is put into the accumulator and printed by calling the print subroutine. Line 510 is a very useful instruction which will decrement the B register and jump to the indicated address as long as the B register is not zero. All we are doing is to output line feeds until the end of the page, and when it is all finished the program jumps to line 610 which calls the change-page subroutine.

Line 530 prints the character, of course, and the next line checks for a carriage return. If it was some other character, this section of the program is finished, and then we can return to the rom program. If



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00100 ; PROGRAM NAME -- INTER
00110 ;
00120 ; INTERFACE PROGRAM FOR TRS-80 AND
00130 ; IBM SELECTRIC I/O PRINTER
00140 ;
00150 ; CONVERTS ASCII CODE
00160 ; TO IBM CORRESPONDENCE CODE
00170 ;
00180 ; USES HARDWARE TO DRIVE
00190 ; SOLENOIDS FROM VARIOUS
00200 ; PORTS LISTED BELOW
00210 ;
00220 ; THE FOLLOWING MEMORY LOCATIONS
00230 ; MUST BE INITIALIZED PRIOR TO USE:
00240 ; POKE 16422 = 00H (ORIGIN L3)
00250 ; POKE 16423 = 7EH (ORIGIN H1)
00260 ;
00270 ; PROGRAM CONTAINS A SUBROUTINE TO ALLOW A
00280 ; CHANGE OF PAPER AFTER 54 LINES
00290 ; BUT BE SURE TO INITIALIZE LINE
00300 ; COUNTER BEFORE LISTING; POKE 16425 = 0
00305 ; AND LINES/PAGE; POKE 16424 = 54
00310 ; WHEN PRINTING STOPS, PRESS 'P' TO CONTINUE
00320 ;
00330 ; THIS PROGRAM USES ANSI ELEMENT
00340 ;
00350 ;
00360 ;
00370 BEGIN LD A,C ;J22560
00380 OR A ;CHAR IS IN C-REG
00390 CP 0BH ;TOP OF FORM?
00400 JR Z,L2 ;JUMP IF 50
00410 CP 0CH ;FORM FEED?
00420 JR NZ,L3 ;JUMP IF NOT
00430 XOR A ;ZERO ACC.
00440 OR (IX+03H) ;IX=025H:LP CONT BLOCK
00450 LD A,(IX+03H) ; IX+3 IS LINES/PAGE
00460 L2 SUB (IX+04H) ;SUBTRACT LINE COUNTER
00470 LD B,A ;INTO B-REG
00480 LD A,0AH ;LINE FEED
00490 L4 CALL ENTRY ;OUTPUT LINE FEED
00500 CALL ENTRY ;CONT. UNTIL FINISHED
00510 DJNZ L5 ;
00520 LD A,L ;
00530 L3 CALL ENTRY ;OUTPUT CHAR
00540 OR 0DH ;CHECK FOR CARR. RET.
00550 RET NZ ;RETURN IF NOT
00560 INC (IX+04H) ;INC LINE COUNT IF CR
00570 LD A,(IX+04H) ;INTO ACC.
00580 CP (IX+03H) ;CHECK END OF PAGE
00590 LD A,C ;GET CHARACTER AGAIN
00600 RET NZ ;RETURN IF NOT END OF PG.
00610 L5 CALL CHGPG ;STOP TO CHANGE PAPER
00620 NOP
00630 RET
00640 ;
00650 ; PORTS AND DELAY TIMES
00660 ;
00670 CHRRPT EQU 07FH ;CHARACTER PORT
00680 CMRPT EQU 0F8H ;CARR. MOVE. PORT
00690 PNTPRPT EQU 0F9H ;PRINT PORT
00700 SHFRPT EQU 0FAH ;SHEET PORT
00710 CRPORT EQU 0FBH ;CARR. RET. PORT
00720 INDRPT EQU 0FCH ;INDEX PORT
00730 SPCPRPT EQU 0FDH ;SPACE PORT
00740 ;
00750 ;
00760 ;
00770 DEL1 EQU 0FFH ;DELAY TIMES
00780 DEL2 EQU 05H
00790 DELTIM DEF5 01H ;DELAY TEMP STORAGE
00800 ;
00810 ; ASCII TO CORRESPONDENCE TABLE
00820 ;
00830 TABLE DEF5 0FFH ;NUL (NULL)
00840 DEF5 0FFH ;SOH (START OF HEADING)
00850 DEF5 0FFH ;STX (START OF TEXT)
00860 DEF5 0FFH ;ETX (END OF TEXT)
00870 DEF5 0FFH ;EOT (END OF TRANSMISSION)
00880 DEF5 0FFH ;ENQ (ENQUIRY)
00890 DEF5 0FFH ;ACK (ACKNOWLEDGE)
00900 DEF5 0FFH ;BEL (BACKSPACE)
00910 DEF5 0FFH ;BS (BACKSPACE)
00920 DEF5 0FFH ;HT (HORIZONTAL TAB)
00930 DEF5 0FDH ;LF (LINE FEED) (INDEX)
00940 DEF5 0FFH ;VT (VERT TAB) (TOP OF FORM)
00950 DEF5 0FDH ;FF (FORM FEED)
00960 DEF5 0FCH ;CR (CARR RET) (CR/LF)
00970 DEF5 0FFH ;SO (SHIFT OUT)
00980 DEF5 0FFH ;SI (SHIFT IN)
00990 DEF5 0FFH ;DLE (DELETE)
01000 DEF5 0FFH ;DCT (DEVICE CONTROL)
01010 DEF5 0FFH ;DC2
01020 DEF5 0FFH ;DC3
01030 DEF5 0FFH ;DC4
01040 DEF5 0FFH ;NAK (NEGATIVE ACKNOWLEDGE)
01050 DEF5 0FFH ;SYN (SYNCHRONOUS IOLE)
01060 DEF5 0FFH ;ETE (END OF TRANS BLOCK)
01070 DEF5 0FFH ;CAN (CANCEL)
01080 DEF5 0FFH ;EM (END OF MEDIUM)
01090 DEF5 0FFH ;SUB (SUBSTITUTE)
01100 DEF5 0FFH ;ESC (ESCAPE)
01110 DEF5 0FFH ;FS
01120 DEF5 0FFH ;GS
01130 DEF5 0FFH ;RS
01140 DEF5 0FFH ;US
01150 DEF5 0FEH ;SPACE
01160 DEF5 7FH ;
01170 DEF5 6AH ;"
01180 DEF5 5FH ;'
01190 DEF5 67H ;%
01200 DEF5 6EH ;&
01210 DEF5 6FH ;'
01220 DEF5 2AH ;!
01230 DEF5 43H ;"
01240 DEF5 63H ;#
01250 DEF5 4FH ;$
01260 DEF5 58H ;%
01270 DEF5 6CH ;^
01280 DEF5 0BH ;_
01290 DEF5 1AH ;.
01300 DEF5 24H ;/
01310 DEF5 66H ;0
01320 DEF5 3FH ;1
01330 DEF5 1BH ;2
01340 DEF5 1FH ;3
01350 DEF5 27H ;4
01360 DEF5 2EH ;5
01370 DEF5 0BH ;6
01380 DEF5 2FH ;7
01390 DEF5 0FH ;8
01400 DEF5 03H ;9
01410 DEF5 6CH ;:
01420 DEF5 2CH ;;
01430 DEF5 6DH ;<
01440 DEF5 1BH ;=
01450 DEF5 5CH ;>
01460 DEF5 64H ;@
01470 DEF5 5DH ;A
01480 DEF5 0EH ;B
01490 DEF5 01H ;C
01500 DEF5 0DH ;D
01510 DEF5 29H ;E
01520 DEF5 20H ;F
01530 DEF5 1CH ;G
01540 DEF5 3CH ;H
01550 DEF5 21H ;I
01560 DEF5 0AH ;J
01570 DEF5 38H ;K
01580 DEF5 09H ;L
01590 DEF5 25H ;M
01600 DEF5 3EH ;N
01610 DEF5 19H ;O
01620 DEF5 26H ;P
01630 DEF5 07H ;Q
01640 DEF5 00H ;R
01650 DEF5 2EH ;S
01660 DEF5 22H ;T
01670 DEF5 35H ;U
01680 DEF5 1DH ;V
01690 DEF5 1EH ;W
01700 DEF5 02H ;X
01710 DEF5 3DH ;Y
01720 DEF5 24H ;Z
01730 DEF5 3BH ;[
01740 DEF5 79H ;\LEFT BRACKET, UP ARROW
01750 DEF5 42H ;]BACK SLASH, DOWN ARROW
01760 DEF5 6EH ;^RIGHT BRACKET, LEFT ARROW
01770 DEF5 69H ;_UP ARROW, RIGHT ARROW
01780 DEF5 49H ;`LEFT ARROW, UNDERLINE
01790 DEF5 54H ;~ACCENT
01800 DEF5 0EH ;A LOWER CASE
01810 DEF5 01H ;B L
01820 DEF5 0DH ;C L
01830 DEF5 20H ;D L
01840 DEF5 29H ;E L
01850 DEF5 1CH ;F L
01860 DEF5 3CH ;G L
01870 DEF5 21H ;H L
01880 DEF5 0AH ;I L
01890 DEF5 3BH ;J L
01900 DEF5 09H ;K L
01910 DEF5 25H ;L L
01920 DEF5 3EH ;M L
01930 DEF5 19H ;N L
01940 DEF5 26H ;O L
01950 DEF5 2EH ;P L
01960 DEF5 08H ;Q L
01970 DEF5 2EH ;R L
01980 DEF5 22H ;S L
01990 DEF5 35H ;T L
02000 DEF5 1DH ;U L
02010 DEF5 1EH ;V L
02020 DEF5 02H ;W L
02030 DEF5 3CH ;X L
02040 DEF5 20H ;Y L
02050 DEF5 3BH ;Z L
02060 DEF5 3AH ;[LEFT BRACE
02070 DEF5 4BH ;]RIGHT BRACE
02080 DEF5 3AH ;^RIGHT BRACE
02090 DEF5 4CH ;_TILDE
02100 DEF5 0FFH ;DEL (DELETE)
02110 ;
02120 ; MAIN PROGRAM
02130 ;
02140 ENTRY PUSH AF ;SAVE AF
LD (CHAR+2),A ;CHAR. INTO 7ECCH
ADD A,80H ;LEGAL CHAR.?
RET NC,START ;JUMP IF 50
POP AF
02190 RET
02200 START PUSH BC ;SAVE ALL REGISTERS
02210 PUSH DE
02220 PUSH HL
02230 PUSH IX
02240 LD IX,TABLE ;LOOKUP TABLE

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continued over page

it was a carriage return, the line count is incremented, and we get the line count and compare it to the lines/page value. In this case it is 54, either placed in this line as an assembly language instruction, or the value poked in the control block before the program was run. If the result turned out to be zero, the zero flag was set, then in line 590 we put the character back into the A register, because this is where the rom expects it to be. The next line will return to rom only if the zero flag was not set, otherwise we jump to the change page subroutine. Line 620 is skipped and we can now return; this part of the program is finished. All this was just to print one character, and it only takes a few hundred milliseconds. Any language other than assembly language simply would take forever.

Now let's continue with the rest of the program and see how it works. This first part, by the way, is basically the same as the program in rom, with a few of our own modifications so it will work for us. The rest of it comes partly from Mr Bateman's program, and from my own efforts. Lines 650 to 790 lists the names and numbers of the ports used, and the delay times for the delay sub-routines used in the program. Line 790 is the delay work area. The ASCII correspondence table, from lines 830 to 2100, is a list of values that is to be interpreted by the program to be output to the printer. We'll see how that's done shortly. The table starts at address 7E37H. Remember, H means hexadecimal. Each address position from that point represents an ASCII character. ASCII character values go from 00H to 7FH,

but we need to translate this into a value our printer can use, which is IBM's own peculiar code. So let's go to line 2140 where it all starts. This is the ENTRY subroutine that was called from the other part of the program, remember? We start by saving the AF register pair, because these registers are to be used by this subroutine and so are PUSHed onto the stack. They will be retrieved just before this subroutine RETURNS. Line 2150 needs some explanation. Look at line 2250. This address is labelled CHAR. Now look at the address 7ECAH, and notice that the hex number at this address is DD, 7ECB is 7E, and 7ECC is 00. Back to line 2150 and see that we are to load the ASCII character in the accumulator into CHAR+2, or in other words, 7ECA+2 or 7ECC. Thus, we have installed the ASCII

```

7E7A D07E00 02250 CHAR LD A,(IX+0) ;START OF TABLE+CHAR
7E7B D07E01 02260 ;NO CHAR?
7E7C D07E02 02270 ;JUMP IF SO
7E7D D07E03 02280 ;SPACE?
7E7E D07E04 02290 ;JUMP IF NOT
7E7F D07E05 02300 ;PRINT SPACE SUBR.
7E80 D07E06 02310 ;FINISHED
7E81 D07E07 02320 ;CR/LF?
7E82 D07E08 02330 ;JUMP IF NOT
7E83 D07E09 02340 ;PRINT CAR RET SUBR
7E84 D07E0A 02350 ;FINISHED
7E85 D07E0B 02360 ;INDEX (LF)?
7E86 D07E0C 02370 ;JUMP IF NOT
7E87 D07E0D 02380 ;PRINT INDEX SUBR
7E88 D07E0E 02390 ;FINISHED
7E89 D07E0F 02400 ;PRINT CHAR.
7E8A D07E10 02410 ;RETURN REGISTERS
7E8B D07E11 02420 ;
7E8C D07E12 02430 ;
7E8D D07E13 02440 ;
7E8E D07E14 02450 ;
7E8F D07E15 02460 ;
7E90 D07E16 02470 ;
7E91 D07E17 02480 ;
7E92 D07E18 02490 ;
7E93 D07E19 02500 ;
7E94 D07E1A 02510 ;
7E95 D07E1B 02520 ;
7E96 D07E1C 02530 ;
7E97 D07E1D 02540 ;
7E98 D07E1E 02550 ;
7E99 D07E1F 02560 ;
7E9A D07E20 02570 ;
7E9B D07E21 02580 ;
7E9C D07E22 02590 ;
7E9D D07E23 02600 ;
7E9E D07E24 02610 ;
7E9F D07E25 02620 ;
7F00 D07E26 02630 ;
7F01 D07E27 02640 ;
7F02 D07E28 02650 ;
7F03 D07E29 02660 ;
7F04 D07E2A 02670 ;
7F05 D07E2B 02680 ;
7F06 D07E2C 02690 ;
7F07 D07E2D 02700 ;
7F08 D07E2E 02710 ;
7F09 D07E2F 02720 ;
7F0A D07E30 02730 ;
7F0B D07E31 02740 ;
7F0C D07E32 02750 ;
7F0D D07E33 02760 ;
7F0E D07E34 02770 ;
7F0F D07E35 02780 ;
7F10 D07E36 02790 ;
7F11 D07E37 02800 ;
7F12 D07E38 02810 ;
7F13 D07E39 02820 ;
7F14 D07E3A 02830 ;
7F15 D07E3B 02840 ;
7F16 D07E3C 02850 ;
7F17 D07E3D 02860 ;
7F18 D07E3E 02870 ;
7F19 D07E3F 02880 ;
7F1A D07E40 02890 ;
7F1B D07E41 02900 ;
7F1C D07E42 02910 ;
7F1D D07E43 02920 ;
7F1E D07E44 02930 ;
7F1F D07E45 02940 ;
7F20 D07E46 02950 ;
7F21 D07E47 02960 ;
7F22 D07E48 02970 ;
7F23 D07E49 02980 ;
7F24 D07E4A 02990 ;
7F25 D07E4B 03000 ;
7F26 D07E4C 03010 ;
7F27 D07E4D 03020 ;
7F28 D07E4E 03030 ;
7F29 D07E4F 03040 ;
7F2A D07E50 03050 ;
7F2B D07E51 03060 ;
7F2C D07E52 03070 ;
7F2D D07E53 03080 ;
7F2E D07E54 03090 ;
7F2F D07E55 03100 ;
7F30 D07E56 03110 ;
7F31 D07E57 03120 ;
7F32 D07E58 03130 ;
7F33 D07E59 03140 ;
7F34 D07E5A 03150 ;
7F35 D07E5B 03160 ;
7F36 D07E5C 03170 ;
7F37 D07E5D 03180 ;
7F38 D07E5E 03190 ;
7F39 D07E5F 03200 ;
7F3A D07E60 03210 ;
7F3B D07E61 03220 ;
7F3C D07E62 03230 ;
7F3D D07E63 03240 ;
7F3E D07E64 03250 ;
7F3F D07E65 03260 ;
7F40 D07E66 03270 ;
7F41 D07E67 03280 ;
7F42 D07E68 03290 ;
7F43 D07E69 03300 ;
7F44 D07E6A 03310 ;
7F45 D07E6B 03320 ;
7F46 D07E6C 03330 ;
7F47 D07E6D 03340 ;
7F48 D07E6E 03350 ;
7F49 D07E6F 03360 ;
7F4A D07E70 03370 ;
7F4B D07E71 03380 ;
7F4C D07E72 03390 ;
7F4D D07E73 03400 ;
7F4E D07E74 03410 ;
7F4F D07E75 03420 ;
7F50 D07E76 03430 ;
7F51 D07E77 03440 ;
7F52 D07E78 03450 ;
7F53 D07E79 03460 ;
7F54 D07E7A 03470 ;
7F55 D07E7B 03480 ;
7F56 D07E7C 03490 ;
7F57 D07E7D 03500 ;
7F58 D07E7E 03510 ;
7F59 D07E7F 03520 ;
7F5A D07E80 03530 ;
7F5B D07E81 03540 ;
7F5C D07E82 03550 ;
7F5D D07E83 03560 ;
7F5E D07E84 03570 ;
7F5F D07E85 03580 ;
7F60 D07E86 03590 ;
7F61 D07E87 03600 ;
7F62 D07E88 03610 ;
7F63 D07E89 03620 ;
7F64 D07E8A 03630 ;
7F65 D07E8B 03640 ;
7F66 D07E8C 03650 ;
7F67 D07E8D 03660 ;
7F68 D07E8E 03670 ;
7F69 D07E8F 03680 ;
7F6A D07E90 03690 ;
7F6B D07E91 03700 ;
7F6C D07E92 03710 ;
7F6D D07E93 03720 ;
7F6E D07E94 03730 ;
7F6F D07E95 03740 ;
7F70 D07E96 03750 ;
7F71 D07E97 03760 ;
7F72 D07E98 03770 ;
7F73 D07E99 03780 ;
7F74 D07E9A 03790 ;
7F75 D07E9B 03800 ;
7F76 D07E9C 03810 ;
7F77 D07E9D 03820 ;
7F78 D07E9E 03830 ;
7F79 D07E9F 03840 ;
7F7A D07EA0 03850 ;
7F7B D07EA1 03860 ;
7F7C D07EA2 03870 ;
7F7D D07EA3 03880 ;
7F7E D07EA4 03890 ;
7F7F D07EA5 03900 ;
7F80 D07EA6 03910 ;
7F81 D07EA7 03920 ;
7F82 D07EA8 03930 ;
7F83 D07EA9 03940 ;
7F84 D07EAA 03950 ;
7F85 D07EAB 03960 ;
7F86 D07EAC 03970 ;
7F87 D07EAD 03980 ;
7F88 D07EAE 03990 ;
7F89 D07EAF 04000 ;
7F8A D07EB0 04010 ;
7F8B D07EB1 04020 ;
7F8C D07EB2 04030 ;
7F8D D07EB3 04040 ;
7F8E D07EB4 04050 ;
7F8F D07EB5 04060 ;
7F90 D07EB6 04070 ;
7F91 D07EB7 04080 ;
7F92 D07EB8 04090 ;
7F93 D07EB9 04100 ;
7F94 D07EBA 04110 ;
7F95 D07EBB 04120 ;
7F96 D07EBC 04130 ;
7F97 D07EBD 04140 ;
7F98 D07EBE 04150 ;
7F99 D07EBF 04160 ;
7F9A D07EC0 04170 ;
7F9B D07EC1 04180 ;
7F9C D07EC2 04190 ;
7F9D D07EC3 04200 ;
7F9E D07EC4 04210 ;
7F9F D07EC5 04220 ;
7FA0 D07EC6 04230 ;
7FA1 D07EC7 04240 ;
7FA2 D07EC8 04250 ;
7FA3 D07EC9 04260 ;
7FA4 D07ECA 04270 ;
7FA5 D07ECB 04280 ;
7FA6 D07ECC 04290 ;
7FA7 D07ECD 04300 ;
7FA8 D07ECE 04310 ;
7FA9 D07ECD 04320 ;
7FAA D07ECD 04330 ;
7FAB D07ECD 04340 ;
7FAC D07ECD 04350 ;
7FAD D07ECD 04360 ;
7FAE D07ECD 04370 ;
7FAF D07ECD 04380 ;
7FB0 D07ECD 04390 ;
7FB1 D07ECD 04400 ;
7FB2 D07ECD 04410 ;
7FB3 D07ECD 04420 ;
7FB4 D07ECD 04430 ;
7FB5 D07ECD 04440 ;
7FB6 D07ECD 04450 ;
7FB7 D07ECD 04460 ;
7FB8 D07ECD 04470 ;
7FB9 D07ECD 04480 ;
7FBA D07ECD 04490 ;
7FBB D07ECD 04500 ;
7FBC D07ECD 04510 ;
7FBD D07ECD 04520 ;
7FBE D07ECD 04530 ;
7FBF D07ECD 04540 ;
7FC0 D07ECD 04550 ;
7FC1 D07ECD 04560 ;
7FC2 D07ECD 04570 ;
7FC3 D07ECD 04580 ;
7FC4 D07ECD 04590 ;
7FC5 D07ECD 04600 ;
7FC6 D07ECD 04610 ;
7FC7 D07ECD 04620 ;
7FC8 D07ECD 04630 ;
7FC9 D07ECD 04640 ;
7FCA D07ECD 04650 ;
7FCB D07ECD 04660 ;
7FCC D07ECD 04670 ;
7FCD D07ECD 04680 ;
7FCE D07ECD 04690 ;
7FCF D07ECD 04700 ;
7FD0 D07ECD 04710 ;
7FD1 D07ECD 04720 ;
7FD2 D07ECD 04730 ;
7FD3 D07ECD 04740 ;
7FD4 D07ECD 04750 ;
7FD5 D07ECD 04760 ;
7FD6 D07ECD 04770 ;
7FD7 D07ECD 04780 ;
7FD8 D07ECD 04790 ;
7FD9 D07ECD 04800 ;
7FDA D07ECD 04810 ;
7FDB D07ECD 04820 ;
7FDC D07ECD 04830 ;
7FDD D07ECD 04840 ;
7FDE D07ECD 04850 ;
7FDF D07ECD 04860 ;
7FE0 D07ECD 04870 ;
7FE1 D07ECD 04880 ;
7FE2 D07ECD 04890 ;
7FE3 D07ECD 04900 ;
7FE4 D07ECD 04910 ;
7FE5 D07ECD 04920 ;
7FE6 D07ECD 04930 ;
7FE7 D07ECD 04940 ;
7FE8 D07ECD 04950 ;
7FE9 D07ECD 04960 ;
7FEA D07ECD 04970 ;
7FEB D07ECD 04980 ;
7FEC D07ECD 04990 ;
7FED D07ECD 05000 ;
7FEE D07ECD 05010 ;
7FEF D07ECD 05020 ;
7FF0 D07ECD 05030 ;
7FF1 D07ECD 05040 ;
7FF2 D07ECD 05050 ;
7FF3 D07ECD 05060 ;
7FF4 D07ECD 05070 ;
7FF5 D07ECD 05080 ;
7FF6 D07ECD 05090 ;
7FF7 D07ECD 05100 ;
7FF8 D07ECD 05110 ;
7FF9 D07ECD 05120 ;
7FFA D07ECD 05130 ;
7FFB D07ECD 05140 ;
7FFC D07ECD 05150 ;
7FFD D07ECD 05160 ;
7FFE D07ECD 05170 ;
7FFF D07ECD 05180 ;

```

character into the byte that represents the IX register's offset. Back to line 2160 for a minute. Here, we add a value to the accumulator that will be sure it is indeed an ASCII character, and if not, will return. Lines 2200 to 2230 make sure that nothing that was in the registers will be affected by our program, and then we are at line 2250. This line will load the accumulator with whatever is at the address formed by adding the IX register with its offset, in this case the address of the table, 7E37H, and the value of the ASCII character. Now the accumulator holds the value of the correspondence code. Line 2260 checks to see if the accumulator holds a character we don't want to print, that is, an FFH. If it is, the program branches to line 2410. Line 2280 checks for a space and will jump to line 2320 if isn't, otherwise it will call the print

space subroutine. The rest of this part of the program works the same, checking for various characters and then branching if it's not the right one. Lines 2410 to 2460 will return all of the registers to their original values and then return. The print space subroutine at line 2500 is the first of our subroutines that actually will send something out to the printer. Here, in line 2500, we get the address of the port labeled SPCPRT, and put it into the C register. The next line will then output whatever value is in the accumulator, in this case FEH, 1111 1110 in binary, to the port whose address is in the C register. This merely turns on the solenoid driver transistor, as indicated in the hardware section. Next, in line 2520, we load a delay value into the accumulator and then jump to the delay subroutine. On

return, we zero-out the accumulator to release the solenoid in line 3560. Next we implement another delay so that solenoid has time to go back to a resting position. These delay times were chosen for my particular printer so that a firm pull-in is realized without multiple spaces being printed. The next subroutine, print carriage return/line feed, is very similar, except that we jump to the carriage movement detection subroutine. Also, the print line feed subroutine works the same. IBM calls a line feed an index. The print character subroutine is a little more involved, so let's examine it. First, in line 2900, we save the character in the E register, then we test the sixth bit of the character to find out if it has a 1 or 0. A 1 indicates an upper-case letter. So in the next line, 2920, we will

jump to line 2980 if there was no shift. Lines 2930 to 2970 is how we output a shift, which by the way has to stay latched until the printing of the character is completed. Now get our character back, line 2980, and latch the character-select solenoids on, 2990-3030, turn on the print solenoid, 3040-3080, turn off the print solenoid, 3100-3110, turn off the character-select solenoids, 3120-3130, and finally turn off the shift solenoid and add a delay, 3140-3190.

The delay subroutine is very simple, and is very handy, so let's look at it. First load into the B register a delay value of FFH, or 255D. This is temporarily PUSHED onto the stack, and then get the value we have been holding in our delay work area, and put it into the accumulator, line 3250. Transfer that value into the B register, and use that handy instruction to decrement the B register as many times as was in the DELTIM address. When that part is finished, POP out of the stack the DELTIM time, decrement it by one, and then jump back to do the whole thing over again. The delay times can be varied, and multiple delays can be implemented to give almost any delay that one desires. A very useful subroutine.

The carriage movement-subroutine at line 3340 is used to check what is happening with the carriage movement detector. First get the port address, and then implement a short delay to give the detector a chance to operate; remember, the program goes through the instructions in microseconds, and the analogue operating detector takes time. Line 3380 inputs the data on the data bus into the accumulator from the port that is addressed by the C register. Line 3390 then tests bit number one, which was D1 in the hardware section, and if this line was low, inverted through the buffer, jump back to test the bit again to line 3380. As soon as a one is detected, we get another short delay and continue.

The change-paper subroutine shows that we can use some of the subroutines in rom if we want to. Lines 3480 to 3510 again saves our registers, and in line 3520 we jump to a subroutine which will input a character from the keyboard. This subroutine is located at 002BH in rom, but I have a subroutine that debounces my keyboard located in another section of memory, so this is where I have to access this subroutine. It deposits the character into the accumulator, so in line 3550 check to see if it is a P. If it isn't, jump back to line 3520 again and again until we have a chance to change the paper. As soon as we input the P from our keyboard, we zero the line counter in line 3570, and finish this part of the program.

That's the whole ball of wax, friends. You can now LLIST those Basic programs in letter-quality printing. However, to use this printer to its fullest, you have to be able to list assembly language programs from the editor/ assembler, and do word processing. To do the first you have to modify the editor/ assembler's print routine, and to do the second you have to have lower-case capability which means you have to modify your computer. You will

also need a word-processor program. (I wrote this article using such a program in Basic which can be purchased from Computronics; it's free if you subscribe to their magazine.) The lower-case modification has been presented in a number of articles, and I won't repeat it here. The program modifications needed to debounce and modify the editor/ assembler's print routine, and to allow normal typewriter-like input when using the lower-case modification, can be purchased from me for \$3 to cover printing and mailing.

I want to make one last point about this interface. If you were to go out and purchase a word-processing system, you would surely spend around three to four thousands of dollars. A hobbyist usually can't justify spending this amount, so a lot of time, a desire to know your computer and the programs that make it work, and the perseverance to stay up 'til late at night chasing bugs, will reward you with a system that has many of the capabilities of the higher priced systems at a fraction of the price. It also can be the way to develop a little income for your efforts. This is helpful when you must justify your expensive hobby. When you have a typewriter that spouts poetry and love letters, you have a cupid's arrow, right to your lover's heart.

### Converting to other computers

Generally this interface can easily be used on other computers, but you need to know your system. You must be able to access the address and data bus of your computer as well as the signals that can produce the equivalent of an out, in, and reset. The out and in signals are usually a combination of the i/o signal and a read or write signal. You will also have to find a five volt supply, either in the computer or by purchasing or building one.

A Z80-based computer has these signals at the microprocessor as IORQ, RD and WR; they may or may not be combined and named as out or in. Other microprocessors have them as well, but their names may be different - check with your computer manual to find out where they are located. The printer port usually has data lines and some control signals, but generally they don't have address lines. Once you know the locations, the next step is to find a connector that will connect to your computers interface port. From this point on, the hardware is the same.

The software may be more difficult to convert. If you are not an assembly language programmer, you may have to find a friend who is. You should also have an editor/ assembler program; without one, conversion may be a long process. A Z80 or 8080 computer will have little problems in conversion. But again, you should be familiar with your own system.

You should know where your normal printer driver is located, and it is essential that your computer is able to use another printer driver. If it can't, only with extreme difficulty and probably with much convoluted coding will you be able to use this interface. So the location that points to your present driver will have to be changed

to point to this new one. If your system has a printer control block which holds this information, the driver address, lines per page count, etc., then there is no problem. If not, you'll have to create one.

Next you will have to be sure that the port addresses in the program will not conflict with any existing ports in your own system. If so, you will have to change some of the hardware logic decoding, but this is easy to do.

Next you'll have to find the routine that checks the keyboard. If you don't know where it is, you'll also have to create its equivalent. This is why you should be very familiar with the inner workings of your system, as well as be able to program in assembly language.

To use other microprocessor based computers requires re-writing all the code to do the same functions as the Z80 code. Here you need to know not only your own microprocessor's assembly language, but also the Z80 code.

## LITERATURE RECEIVED

Could Activair have issued data sheets describing a range of zinc-air button cells which are said to offer long life, high energy density, constant output and extended shelf-life. Suggested uses range from hearing-aids to security systems. Gould Activair UK, 11 Ash Road, Wrexham Industrial Estate, Wrexham, Clwyd LL13 9UF. WW400

The 1983 catalogue from Lambda describes the company's range of power semiconductors and d.c. power supplies. There are many pages of application notes. Lambda Electronics Co., Abbey Barn Road, High Wycombe, Buckinghamshire. WW401

The Zevac range of desoldering tools includes hand-held tools capable of removing multipin devices even from multi-layer printed circuit boards. For static-sensitive mos devices there is a low-voltage model powered via an isolating transformer. Further information from Tony Chapman Electronics, Electron House, Hemnell Street, Epping, Essex CM16 4LS. WW402

The latest edition of the RS Components catalogue has over 400 pages. Among many new products are a speech-synthesis system, a 13A mains plug incorporating an earth leakage circuit-breaker, ferrite cores for switch-mode power transformers, a wideband 50 ohm r.f. amplifier i.c. and an insulation-displacement wiring system. RS Components Ltd, P.O. Box 427, 13-17 Epworth Street, London EC2P 2HA. WW403

# COMMUNICATIONS

## Cellular satellite

While the UK is planning the introduction of terrestrial, mobile, cellular-radio systems for areas of high population density, NASA has been petitioning the FCC to reserve frequencies and define conditions for a satellite-assisted cellular system that would be capable of covering large, thinly-populated rural areas using frequencies between 800 and 900 MHz. NASA, in association with the Canadian government, plans to launch an experimental MSAT-X in 1987 using 821-825 MHz and 866-870 MHz. This would have a 10-metre u.h.f. aerial providing six spot beams, four directed at Canada and Alaska, two at the USA.

The satellite would augment urban terrestrial cellular-type systems, but it would be used only by mobiles outside the range of ground-based transmitters. The main data base in which mobile locations are stored would direct calls via satellite where appropriate. Terrestrial networks would have microwave feeder links with the satellite.

Japanese firms are beginning production of 900 MHz compact transceivers for the new "personal radio service", and one way and another it looks as though 800-900 MHz will soon be heavily used for mobile and personal radio systems.

## Microwave or u.h.f.?

Where does the "microwave" spectrum begin? It is agreed internationally that the boundary between v.h.f. and u.h.f. falls at 300 MHz (1-metre), but most of us would consider that only systems above 1000 MHz (1 GHz or 30 cm wavelength) should be described as microwave systems.

My reason for raising this subject is not purely academic: I notice that Marconi Communications Systems proclaimed February 11, 1983 as the Golden Jubilee of "the world's first commercial microwave communications link". This was the 15-mile link between the Vatican and the summer residence of Pope Pius XI at Castel Gandolfo, opened in February 1933, following several years of investigation by Marconi of duplex telephony systems working on wavelengths below one metre.

This pioneering work was undoubtedly important and a notable world "first". But it has always been my understanding that these systems used wavelengths of about 50 cm, in other words about 600 MHz. Hence my quibble about "microwave", particularly in view of the similar anniversary two years ago of the STC (ITT)

"microray" link across the English Channel. This was demonstrated in March 1931 using a wavelength of about 18 cm (about 1.7 GHz) - admittedly an "experimental" link. Perhaps, also, we should not forget that it was Barkhausen and Kurz whose work on electronic oscillators resulted in the early magnetrons that pioneered centimetric radio from about 1919. Nevertheless, in 1933 Marconi *did* achieve another "first" that proved of great importance in the study of v.h.f. and u.h.f. propagation. This was when he received 57 cm (525 MHz) transmissions at a distance of 168 miles and so conclusively demonstrated that tropospheric bending meant that signals on these frequencies were not, as previously believed, limited to the optical line-of-sight.

## Higher radar

Today, for some applications, interest has shifted from microwave to millimetric systems. The ability to achieve highly directional beams with aerials only a few inches in diameter is leading to the development of 94 GHz radar systems for missile guidance, although details of American and British systems tend to be restricted. The attraction of frequencies between about 80 and 110 GHz is that they fall in the low-attenuation "window", and can penetrate fog and dusty atmospheres. But the hardware is not easy or cheap.

The U.S. services are also currently making a great bid for "new technology" in the form of multi-mode airborne radar that could be used as an advanced all-weather guidance control ("Joint Stars") for both fighter aircraft and multiple missiles for attacking scattered armoured formations. However US Congress has denied further funds for the tactical communications system "Seek Talk" claiming it overlapped with the alternative multi-billion-dollar (JTIDS) (Joint Tactical Information Display System).

## Early digits

Most of us consider "spread-spectrum" techniques using digitally-encoded speech as one of the main communications development areas of the past few years. Spread-spectrum can offer anti-jamming, anti-interference, anti-intercept properties as well as selective addressing, accurate timing and high-resolution radar. It came as something of a shock, therefore, to read a recent account by William R. Bennett ("Secret telephony as a historical example

of spread-spectrum communications" *IEE Trans on Communications* Vol Com 31, No 1, January 1983) of the American wartime system known as "Green Hornet" or "Sig-saly" which provided secure digital speech over long-distance h.f. radio links during the latter part of World War 2. In this system, the bandwidth of the basic speech signal was first reduced by a vocoder, then the vocoder output was sampled and quantized to base six and a random, one-time, six-valued key stream added modulo six to obtain a public message that was conditionally secure against anyone not in possession of the key sources. The coding and decoding key sources consisted of identical disc records used once only and then destroyed. Each disc provided 15-minutes of speech and was delivered by courier. The terminals included a self-destruct feature and were installed at Washington DC, London, Paris and in North Africa, Hawaii, Australia and the Philippines. It was well known that German cryptanalysts succeeded in breaking the more conventional transatlantic scrambling system and listened to some of the Churchill/Roosevelt conversations, but Green Hornet was totally secure though clearly a costly system with its couriers and random, rather than pseudo-random, key streams.

Nevertheless Bennett shows that this 50 year-old system developed by Bell Telephone Laboratories achieved a remarkable string of "firsts": first unbreakable enciphered telephone; first quantized speech; first p.c.m. speech; first multilevel f.s.k.; first useful realisation of speech bandwidth compression; first use of f.s.k./f.d.m. as a viable transmission method over a fading medium; first use of multilevel "eye pattern" to adjust sampling intervals.

The vocoder was designed for male voices but the system coped with Eisenhower talking to his wife, though one notes from the transcripts that Winston Churchill was sometimes eager to hand over the phone to his secretary on the grounds of his increasing deafness!

# AMATEUR RADIO

## Hazards?

The National Radiological Protection Board has recently published a new Consultative Document containing proposals

# COMMENTARY

for common European limits for maximum exposure to non-ionizing radiation at e.l.f., r.f. and microwave frequencies. Comments have been invited by July 1, 1983.

Brian Johnson, G3LOX, has drawn attention to a potential fire hazard arising from the ageing of tightly-laced, multi-cable wiring harnesses using p.v.c.-insulated wires. It appears that after 15 to 20 years there is a tendency for the p.v.c. insulation to dry out, harden and become brittle with the result that the lacing may bite into the p.v.c. In this case, this caused a short-circuit of the 12-volt heater supply leads in a 1960s h.f. transceiver. This resulted in a small fire. Although this was quickly extinguished it could have been much more serious if the equipment had been unattended at the time. It is not uncommon practice, with older equipment, to switch on some time before it is used in order to overcome the initial, warm-up, frequency drift. There is still a lot of equipment in use over 15 years old.

## Man-made problems

It is not only in the UK that amateurs are finding that the problem of operating a radio station in a residential or urban area appears to be returning to the levels experienced in the days of v.h.f. television in the 1950s and 1960s, with all the consequent social problems that ensue. The poor electromagnetic characteristics of the combined television set and video recorder, of unit audio, the greater sensitivity of viewers in the face of the large number of cases of interference caused by c.b. transmitters (still not far short of a 1000 per week), leaky cable tv systems, the difficulty of obtaining planning permission for aerial masts in some areas; all such factors are contributing to a growing feeling of unease. A recent editorial in the ARRL journal *QST* comments: "increasingly radio amateurs find themselves embroiled in legal action arising from zoning and radio interference conflicts. Within the past decade the number of local statutes seeking to restrict our right to erect antennas - and in some cases to operate at all - has increased manifold."

Some American amateurs are finding it necessary to resort to "invisible" or hidden aerials. One technique is to use thin (24 to 26 gauge) enamelled wire supported by nylon kite string to provide "hard to see" aerials. An alternative technique is to use a wire concealed in an innocent-looking clothesline or in a flag pole, or to use a

television or v.h.f. aerial and its associated feeder cable as a long-wire aerial.

## Here and there

The Home Office is seeking to reduce the chances of successful impersonation of candidates taking the amateur Morse test, whereby an experienced operator presents himself as the candidate. In future all candidates will be required to show a valid passport or produce some other positive means of identification when taking the test. That some other curious practices are coming into the hobby became apparent in 1981 when a much-publicised "DX-pedition" by an American amateur to St Felix Island (during which 800 contacts were made) has since been proved to have been an elaborate spoof, although supported by a number of carefully forged documents. It is now known that the amateur concerned never set foot on the island but operated from the Chilean mainland.

The use of lead-acid car batteries to power 12V solid-state transceivers from a fixed location normally involves the risk of damage caused by acid-spillage, as well as being a rather messy business. Many of the problems may be overcome when the Chloride company markets their Exide Torquestarter range of batteries in the U.K. These batteries, with built-in carrying handle, are already marketed in Australia and South Africa but seem unlikely to be available in the U.K. until next year. They are totally sealed, do not require topping up and cannot spill or leak acid. They use a "recombination electrolyte" with no free acid and with the electrolyte held in sub-micron glass wool. Frank Harris, G4IEY has been using one acquired in Australia and finds it a satisfactory, house-trained power source at lower cost than a heavy current mains power supply unit. It is kept charged from a simple, low-cost mains charger.

There were about 45,000 amateur licences in force in the UK at the end of 1982, compared with about 18,500 at the end of 1972. Main increase has come in the form of Class B v.h.f. only licences which do not require a Morse test. Whereas in 1972 there were approximately four Class A licences to every one Class B, there now appear to be significantly more Class B than Class A, and the gap is widening all the time.

In South Africa it has been the practice to restrict new amateurs to the use of c.w. for the first year of operation (as was done in the UK some thirty years ago). This rule is now being amended so that an amateur

can use telephony after furnishing proof of establishing 200 contacts using Morse.

## In brief

The newsletter of the "DX-TV" group of enthusiasts interested in long-distance television reception has been revived by Dave Launder (18 Burnside Close, Barnet, Herts EN5 5LN) and a copy is available on request provided that a stamped addressed envelope is sent to him. Among the topics covered in the Winter issue are the problem of interference to Band 1 reception caused by visual display units, the question of the future use of Band 1 frequencies, auroral propagation and the use of monitor receivers with scanning facilities. . . . A terrestrial linear transposer repeater, similar to those used on amateur satellites, has been tried at Dunedin, New Zealand. It can cope with several transmissions simultaneously (but involves power sharing) and is reported to result in less flutter on f.m. signals as well as handling s.s.b. transmissions. . . . The number of stations equipped for 144MHz earth-moon-earth "moonbounce" operation is increasing with contacts being made by stations having output down to about 100 watts. Clive Penna, G3POI recently became the second station in England to "work all continents" on 144 MHz as a result of using this mode. . . . The FCC is considering the elimination of all licensing for c.b. operation. . . . Trans-equatorial propagation during August 1982 result in a 144MHz two-way contact between ZC4G0 in Cyprus and Z22JV in Harare, Zimbabwe, a distance of about 4000 miles. Power at the Cyprus end was only 60 watts. . . . A new beacon on 28.208MHz with the callsign WA1IOB is located at Marlborough, Mass., U.S.A. and has an output of 20 watts to an omni-directional aerial. . . . Mobile rallies in May include: Maidstone Y Sportscentre, Melrose Close, Cripple Street, Loose Road, Maidstone on May 1; Lincolnshire Showground, 4 miles north of Lincoln (A15) on May 8; Northern Mobile Rally, Great Yorkshire Showground, Harrogate and the Swindon rally at Park School, Marlowe Avenue, Swindon both on May 15; Welsh Amateur Mobile Rally, Memorial Hall, Barry on May 22; East Suffolk Wireless Revival, Civil Service Sports Ground, Bucklesham, near Ipswich on May 29. . . . The US Congress finally approved Treaty Document 97-21 at the end of 1982 thus making possible the ratification of the Radio Regulations as agreed at W.A.R.C. 1979.

PAT HAWKER, G3VA

# Semiconductor noise analyser

Measures voltage and current noise densities of devices from 0.1Hz in decades to 10KHz.

A brief summary of the noise sources is given here; for more detailed information the reader is referred to the literature contained in References 1 to 5. The three main sources are:

- Johnson noise, which arises from the thermal agitation of the charge carriers and leads to a noise voltage  $v_n = \sqrt{4kTBR}$  in a bandwidth B across resistance R;
- shot noise, which is brought about by the discrete nature of the charge carriers giving rise to a noise current  $i_n = \sqrt{2eIB}$  where e is the electronic charge and I is the mean current flow;
- flicker (1/f) noise, which dominates the low-frequency behaviour, its spectral noise density increasing as 1/f. It is largely due to surface defects in semiconductors.

In junction fets (Fig. 1(a)), there is Johnson noise in the resistive (source-drain) channel, of order  $\sqrt{4kT/g_m}$  per root Hertz. There will also be shot noise in the gate current,  $i_n = \sqrt{2eI_g}$ . Since  $I_g$  is typically a few pA,  $i_n$  is extremely small (0.01pA).

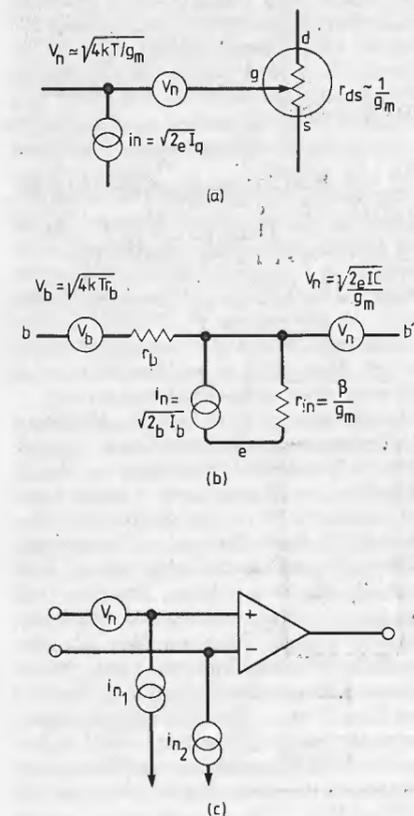


Fig. 1. Noise models of a fet(A), a bipolar transistor(b) and an op-am(c).

by Ian Marshall and John Brydon

In bipolar transistors (Fig. 1(b)), shot noise in the base current is developed across the input resistance ( $r_{in} = \beta/g_m = \beta r_e$ ). Shot noise in the collector current is represented by an equivalent noise voltage at the base ( $v_n = i_n/g_m$ ), and there is a further contribution from Johnson noise in the base resistance  $r_b$ . At low frequencies (<100Hz) flicker noise becomes significant.

All resistors generate Johnson noise, and, apart from wirewound and bulk metal types, there is an additional contribution arising from the granular nature of the

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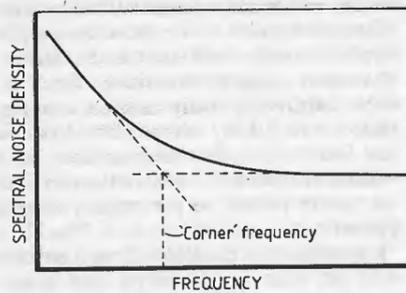


Fig. 2. Spectral noise density of typical op-amp.

resistive material. This last contribution is expressed in microvolts per volt applied across the resistor, in a specified bandwidth.<sup>6</sup>

## Noise characterization

The information required for a full noise characterization of a semiconductor device is the spectral density as a function of frequency. The total noise is then found by integration of the spectral density over the relevant bandwidth. Unfortunately, these figures are not always readily available from manufacturers' data sheets. For example, it is quite common for a noise figure (in dB) to be given without clearly specifying the bandwidth or source impedance appropriate to the measurement.

Furthermore, a broadband figure intended for audio-frequency users can be highly misleading for low frequency (<100Hz) design calculations, as Fig. 2 illustrates.

This shows the form of the voltage (or current) spectral noise density (s.n.d.) of a typical op-amp (see also Fig. 1(c)). At higher frequencies, the s.n.d. is independent of frequency and relatively low in amplitude; this is referred to as the "white noise" region. However, at lower frequencies the s.n.d. rises as the frequency decreases, following a 1/f law. The intersection of the asymptotes, the "corner" frequency, should usually fall below the signal frequency: otherwise noise can become troublesome in critical applications. The lower the s.n.d. amplitude in the "white noise" region, and the lower the corner frequency, the better the op-amp can perform as a low-level amplifier.

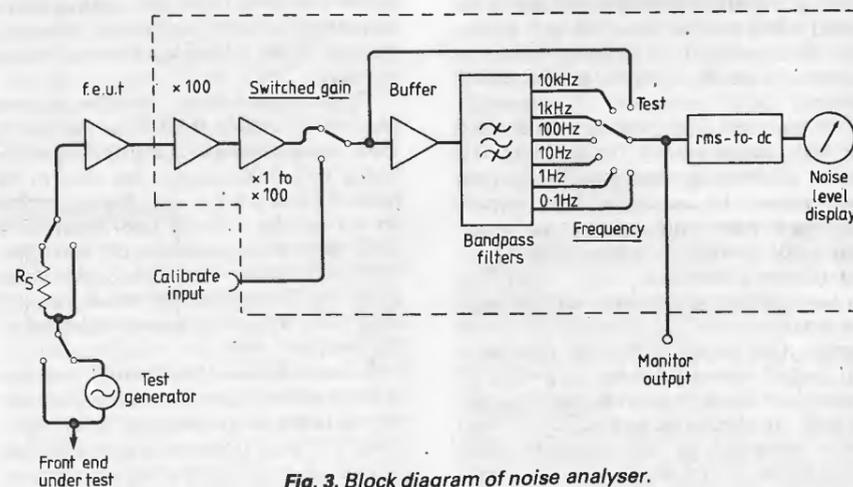


Fig. 3. Block diagram of noise analyser.

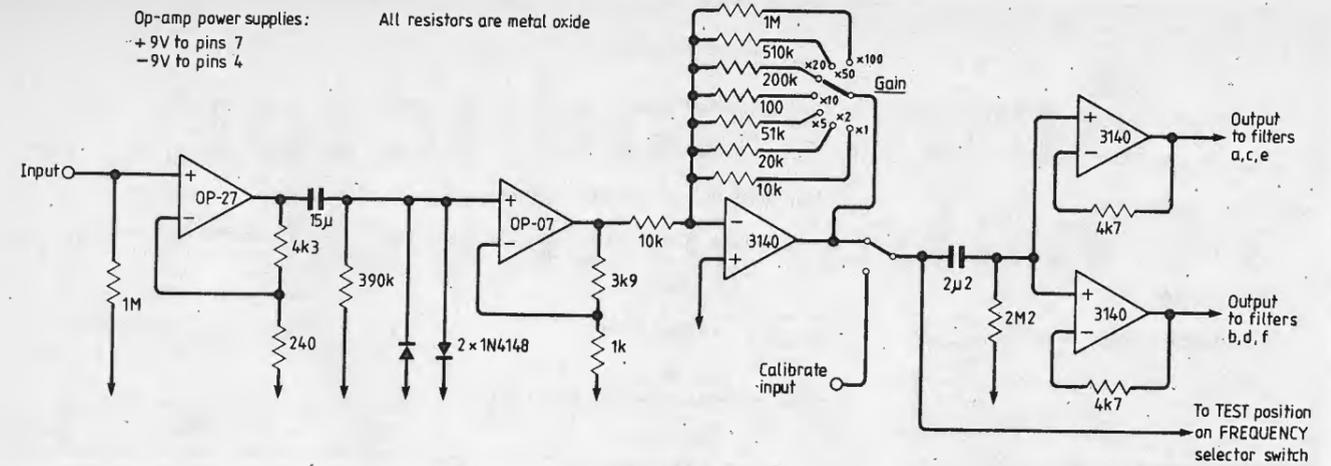


Fig. 4. Three-stage preamplifier, gain-switchable from 100 to 10,000.

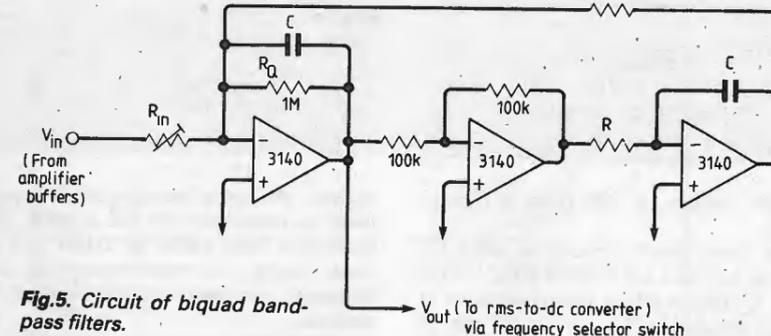


Fig. 5. Circuit of biquad band-pass filters.

Typical figures are  $20nV/\sqrt{Hz}$  and 30Hz (quoted by Signetics for the 741)<sup>7</sup> compared with  $3nV/\sqrt{Hz}$  and 2.7Hz (the manufacturer's noise voltage for the OP-27)<sup>8,9</sup>.

The noise analyser enables the s.n.d. to be measured at spot frequencies of 0.1Hz and decades to 10kHz. The circuit under test can be configured to allow its voltage noise and current noise to be studied separately.

Figure 3 shows the noise analysis system. Connected to the circuit under test, it consists of a low-noise preamplifier stage with fixed gain, followed by a switchable gain stage and a bank of band-pass filters feeding the r.m.s.-to-d.c. converter circuitry. The source resistance  $R_s$  may be shorted out to allow measurement of the front end noise voltage. With  $R_s$  in circuit, the resulting noise is the r.m.s. sum of voltage, current and resistor noise:

$$V_r^2 = V_n^2 + i_n^2 R_s^2 + V_{R_s}^2 \quad (1)$$

## Circuit function

The test circuit output is taken to a pre-amp, shown in Fig. 4, which has as its first stage an OP-27 ultra-low-noise op-amp. This is followed by two further gain stages and buffers, which altogether provide a voltage gain switchable from 100 to 10,000 in 1, 2, 5 steps.

The amplified noise "signal" from the front end is passed to six "biquad" band-pass filters, having centre frequencies of 0.1 Hz, 1Hz and successive decades to 10 kHz. The bandwidths and passband gains of the filters are scaled such that the gains

decrease as the square root of bandwidth; the requirement for equal amplitude outputs when fed with broadband white noise. To arrive at spectral noise density figures it is thus possible to divide all six outputs by the same constant and obtain directly readings in terms of  $nV/\sqrt{Hz}$ .

The filter outputs are selected as required by a rotary switch and applied to an r.m.s.-to-d.c. converter which drives a meter calibrated directly in spectral noise density, with a full scale of  $100\mu V/\sqrt{Hz}$ . This reading is divided by the gain switched in (between 1 and 100) to arrive at the noise present at the noise analyser input socket.

A seventh position (TEST) of the frequency selector switch allows the noise from the preamplifier to pass directly to

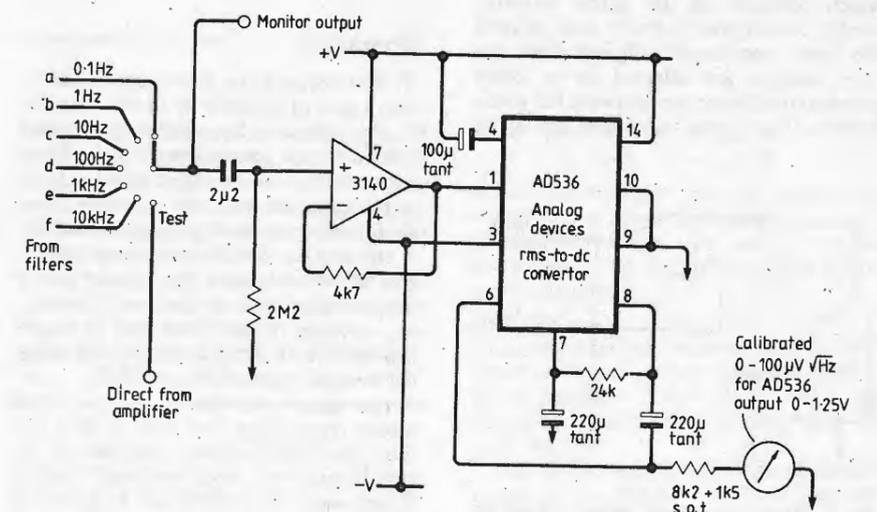


Fig. 6. R.m.s-to-d.c. converter. Response is flat within 2% from 0.1Hz to 60kHz.

### Specification

Input range for full output	100µV-10mV rms	broadband noise
Maximum input offset	±250mV	
Input impedance	1MΩ hard-wired; normally shunted	see text
Output reading	Full scale 100µV/√Hz (r.m.s.)	Divide by gain setting
Switchable gain	1,2.5,10,20,50,100	
Calibration input	(unity gain)	a.c.-coupled
Measurement frequencies	0.1 Hz and decades to 10kHz TEST: Broadband (-3dB at 21 kHz) (Full scale 1.25V r.m.s. in this mode)	
Monitor output	Input to r.m.s.-to-d.c. convertor brought out	
Internal preamp noise, input grounded	8nV/√Hz 8nV/√Hz 20nV/√Hz 80nV/√Hz	100Hz 10Hz 1Hz 0.1Hz
Power supply	Two "PP9" batteries	Current drain ~ ±100mA

completed by an inverting stage with gain switchable from 1 to 100 in 1,2,5 steps, and dual buffers after further a.c.-coupling to remove any d.c. offsets.

**Bandpass filters.** The biquad type of filter allows the various parameters to be easily selected. Referring to Fig. 5, the centre frequency,  $\omega_0$ , is  $\omega_0 = 1/RC$ , the  $Q$  (-3dB) is  $R_Q/R$  and the passband gain  $G$  is  $R_Q/R_{in}$ . Each of the six filters comprises two integrators and an inverter in a loop, which combination behaves as a parallel tuned circuit with an artificial inductance  $L$  given by  $R^2C$ . The calculated  $Q$  ( $R_Q/R$ ) gives the -3dB bandwidth as  $f_0/Q$ , and the effective bandwidth for white noise is  $\pi/2$  times this (found by integration of the filter transfer function over all frequencies).<sup>10</sup>

Filter gains are set to assist in making spectral noise density measurements. The product of passband gain and square root of effective bandwidth is set at  $100\sqrt{\pi/2} = 125$  for all six filters.

**R.m.s.-to-d.c. converter.** This is based around an Analog Devices AD536 chip, which contains all the active circuitry needed to compute the true r.m.s. value of the input waveform<sup>11</sup>. Signals from the filter outputs are selected by a rotary switch and buffered before being fed to the AD536. The circuit used here has a flat

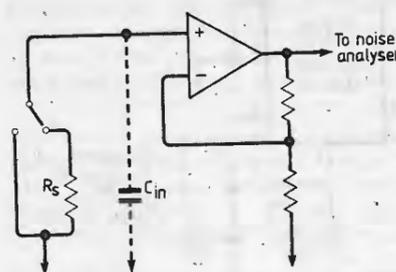


Fig. 7. Measuring noise density of an op-amp.

response within ± 2% from 0.1Hz to 60kHz.

The meter reads directly in  $\mu V/\sqrt{Hz}$  true r.m.s. with a full scale of  $100\mu V/\sqrt{Hz}$  r.m.s. Output levels at the frequencies of interest are divided by the overall gain of the circuit on test and the noise analyser switched-gain stage (1 to 100), to arrive at the equivalent input noise density of the device under test (usually expressed in  $nV/\sqrt{Hz}$  for voltage noise and  $pA/\sqrt{Hz}$  for current noise).

### Calibration

Each filter input resistor ( $R_{in}$  in Fig. 5) is made variable to aid calibration. If a broadband noise generator of known spectral noise density is available, then this can be used to set up the filters. Otherwise, the best method is to measure the -3dB points and then scale the peak gains accordingly: that is,  $Gain = 100/\sqrt{B_{-3dB}}$ . The "CAL IN" socket provides buffered unity gain to the filters, the gain control being inoperative if this is selected.

### Operation

(1) The device to be investigated is set up with a gain of typically 20 to 100. (see Fig. 7). For op-amps, the non-inverting configuration is most convenient since the source resistance ( $R_s$ ) can be varied independently of the gain. As with any amplifier stage, the following precautions must be taken:

- the gain-bandwidth product of the device should not affect the selected gain at the measurement frequencies of interest;
- screening of the front end is recommended for all measurements, and essential for high values of  $R_s$  (>100kΩ);
- the input capacitance of the circuit layout (typically a few tens of pF) may limit the high-frequency response of the circuit under test when very high values of  $R_s$  are used. This effect can be tested by applying a sinusoidal signal in series with

$R_s$ , and sweeping through the frequency range to investigate the fall in gain. This factor can then either be taken into account during noise measurements, or measurements can be restricted to lower frequencies.

(2) Select  $R_s=0$  by shorting the source resistor to ground. This enables the input noise voltage to be measured.

(3) To avoid overloading the first stage of the noise analyser, check with an oscilloscope that the broadband noise output is in the range  $100\mu V-10mV$  (r.m.s.), and that the d.c. offset at the output is less than ±250mV.

(4) Connect the test circuit to the Input socket of the noise analyser, and switch the gain control to the minimum.

(5) At each selected frequency, the gain control is adjusted until the Monitor Output signal is in the range 1-4V pk-pk. It will then be necessary to wait about 20 seconds, the time constant of the AD536 circuit, before a reading can be taken. At 10Hz and below the reading will be seen to fluctuate due to the lower frequency components of the noise, and an average must be taken "by eye".

(6) This completes the readings necessary for an analysis of the noise voltage.

(7) Now switch in a source resistor  $R_s$  to obtain noise levels at least twice as large as before, and so enable separation of the voltage and current contributions: 100kΩ is suggested as an initial value. Devices with very low current noise (e.g. fet op-amps) will require larger values (but see precautions above regarding input capacitance). Wirewound resistors are recommended as they produce no significant component noise above the thermal contribution. The front end output offset should always be less than ±250mV, and it should be shielded to eliminate mains interference.

(8) Step 5 is repeated with  $R_s$  in circuit.

(9) Steps 7 and 8 can be repeated with different values of  $R_s$  as required.

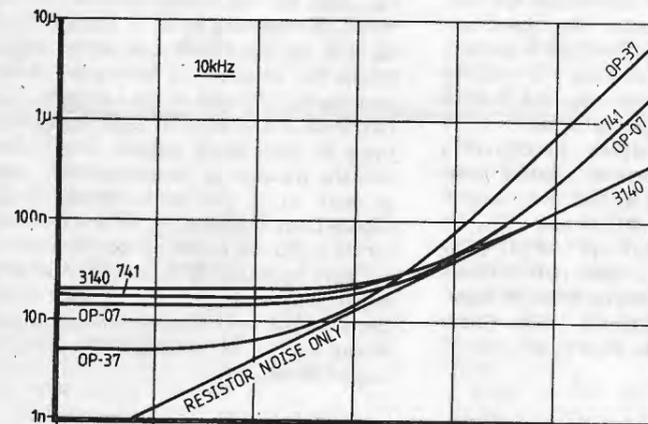
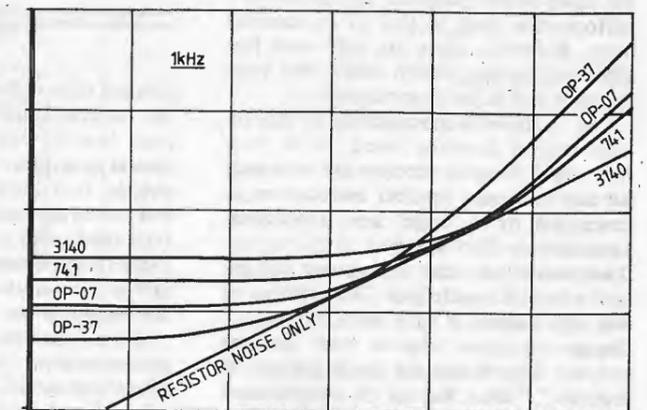
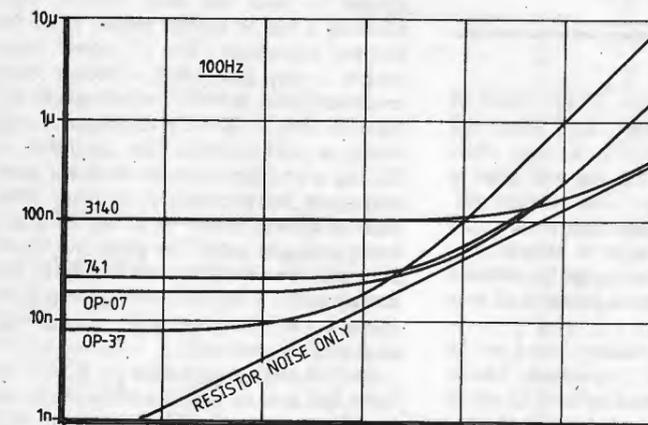
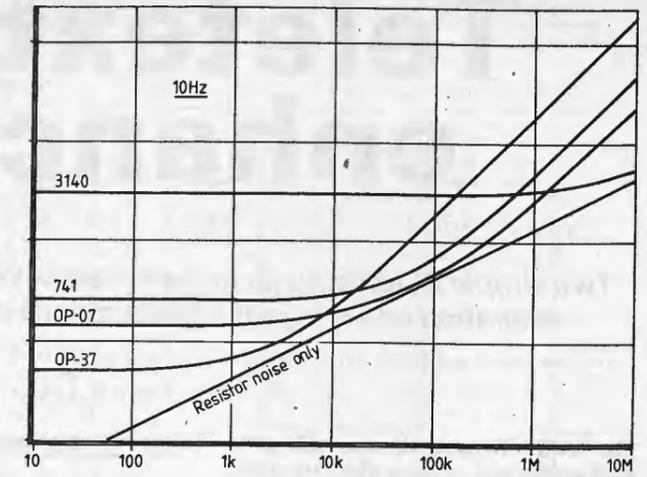
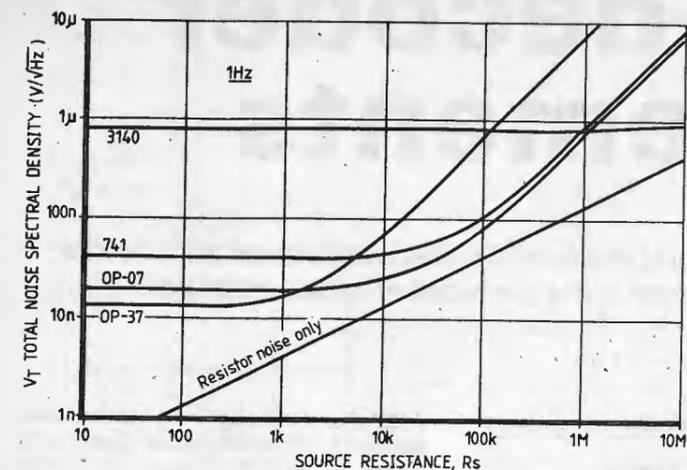


Fig. 8. Spectral noise densities of four op-amps and a resistor plotted at frequencies from 1Hz to 10kHz.

### Analysis

Each meter reading of spectral noise density is referred to the input of the device under test by division by the noise analyser switched gain (1 to 100) and by the test circuit gain itself. For an example, an OP-37 with circuit gain 50, noise analyser gain 100, gave a reading of  $20\mu V/\sqrt{Hz}$  at 10kHz.

$$V_n \text{ for OP-37 at } 10kHz = \frac{20\mu V/\sqrt{Hz}}{50 \times 100} = 4nV/\sqrt{Hz}$$

This division is carried out on each of the readings made, to arrive at the spectral

noise densities. The results with  $R_s=0$  give the input noise voltage ( $v_n$ ) directly\*. With  $R_s$  switched in, the observed s.n.d. ( $v_T$ ) is the r.m.s. sum of the voltage noise ( $v_n$ ), the source noise ( $v_{R_s}$ ) and the current noise ( $i_n$ ) developed across  $R_s$ .

We take as the source noise ( $v_{R_s}$ ) the thermal noise of a resistance, namely  $\sqrt{4kTR_s}$  per root Hertz. At room temperature the following figures apply: 10k-ohm, 13nV/√Hz; 100k-ohm, 41nV/√Hz; 1M-ohm, 130nV/√Hz. Hence for a given

\*Neglecting the input noise of the noise analyser itself, which can be taken into account using the specification, if so desired, for critical measurements.

$R_s$  we perform the calculation

$$i_n = (v_T^2 - v_n^2 - v_{R_s}^2)^{1/2}/R_s$$

at each frequency to find the appropriate current noise spectral density.

Tabulated values of  $v_n$  and  $i_n$  may be plotted as in Fig. 1, or as described below under Results.

### Results

The noise analyser has been used to characterise several commonly-used operational amplifiers. Values of  $v_n$  and  $i_n$  are measured as a function of frequency for each device.

One of the most useful forms of presentation of the results is as log-log graphs showing total noise voltage ( $v_T$ ) versus

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# Teletext decoder enhancements

Two simple modifications to the Wireless World decoder are described which enhance its operation and brings the performance closer to the standard of commercial units.

The W.W. Teletext Decoder still gives good service and, to those who have added the subsequent modifications to provide the more recent facilities, has provided a performance close to that of commercial units. However, there are still some features outstanding which could ease page selection and improve acquisition.

Fig. 1 shows a modification to the remote control decoding board (W.W. May '79) which simply removes the necessity for any new page number selection to be preceded by a 'Page' key depression. Operation is then identical to that of the Time mode (in terms of numeric key entry) which is unaffected. The number of key depressions is thus reduced and, to change magazine number only involves two key depressions e.g. from 100 to 200 requires '2' then 'Reveal'. A 4 input nand gate detects the presence of the first digit (i.e. magazine number) of the new page number and simulates the reception of a 'Page' command by taking 314(6) high via 323(2) for the duration of the Data Allow clock pulse at 314(6). At the end of the pulse this condition is clocked into IC310 by the negative edge of the simulated e.o.c. pulse present at 323(6) which increments the write-address from 00 to 01. This is then followed by a pulse at 304(22) which clocks the received digit into IC312, and finally the e.o.c. pulse at 304(24) increments the write-address in the normal way. Thus reception of the first digit, say 1, gives rise to a display of P1XX and the next two digits are entered in the normal way. The two additional ICs required are IC322 (74LS20) and IC323 (74LS00) and are most conveniently mounted between the first two rows of ICs on the remote control board.

Fig. 2 shows a simple addition to the remote control decoding board which generates the following functions:-

(i) a 10 second cut-box pulse during row 0 following either any key depression (with the exception of TV) or upon detection of the selected (sub) page. This eases page selection since the normal tv picture may still be viewed whilst a new page or time is keyed in, and an indication is given when the page has been acquired. Also, by pressing 'Spare' for example, the status of the selected page, or real time clock, may be observed without intruding unduly into the tv picture.

(ii) a clear-page pulse is generated following the initial detection of a newly

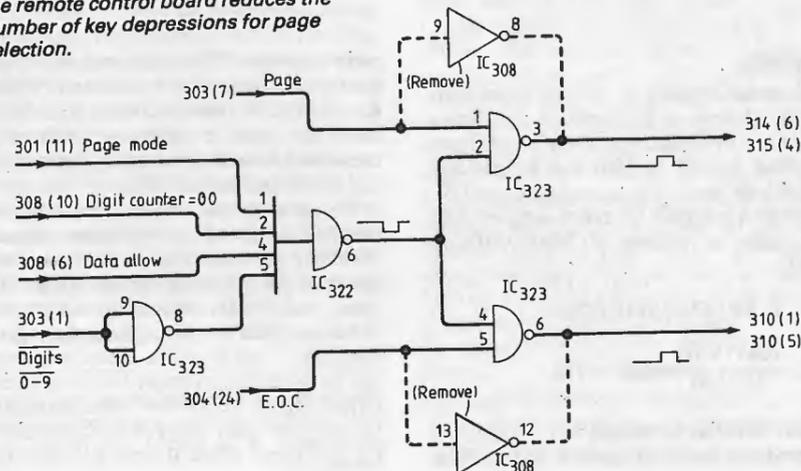
by K. Drew

selected time-coded page. This is based on the general requirement that when the page headers stop rolling a clear cycle should take place before the new page is written into memory. This strategy enables us to initiate a page clear cycle in the time mode which cannot be simply provided by the normal clear page bit detector and is most useful when being used as a sub-page selector.

(iii) a sound mute facility, based on the remote control 'Spare' command. This is gated with the 10 second pulse of (i) which minimises the risk of accidentally muting the sound as two key depressions are then required for this function. The 'Spare' key may then be labelled 'S' which is pressed once for 'Status' (revealing the cut-box information of (i)) and twice for 'Sound Mute' which has a toggling action.

Operation is as follows. Receipt of a correctly decoded remote control command triggers the 10 second timer output (403,6) via (305,3), (402,3) and (401,10). Triggering also occurs via (402,2) when (78,6) goes high (i.e. stop roll headers), indicating that the newly selected page/time has been detected. The timer output is gated with Row 0 at (402,10)

Fig. 1. Simple additions and removals from the remote control board reduces the number of key depressions for page selection.



and, after buffering, sets the 'cut-box' latch at (51,10) which enables Row 0 to be viewed in the tv/Text mode. Tr 1 is included to reset the timer period, thus allowing a full 10 second display from the last key depression. The 10 second timer output is also gated with a 100ms spare command pulse at (402,4) which clocks the bistable (404,3). A buffered output is provided at (401,15) with the capability of driving a t.t.l input. In the author's unit, two spare open collector invertors were used to drive a green 'Mute on' led and a spare analogue gate. The pulse at (401,6) also sets the clear page latch (78,10) following either a remote control Clear command at (307,9) or when (78,6) goes high as described previously.

If a 556 dual timer is used for IC403, the spare half may be usefully employed in the astable mode to provide a constant 1600 Hz clock for the remote control decoder board, as suggested by R. T. Russell. Note the use of the 4049B hex buffer which avoids the necessity of having to replace existing IC's 51 and 78 by 1.s types. The circuit of Fig 2 may be built on a small piece of vero board approx. 5cm x 10cm and the number of interconnection, may be kept to 13 (including power) if the diodes from IC20 and IC306 are mounted on the underside of their respective i.cs.

I have found the WW Teletext decoder a useful and challenging project and would like to thank J. F. Daniels for the original design and all the other authors for their contributions.

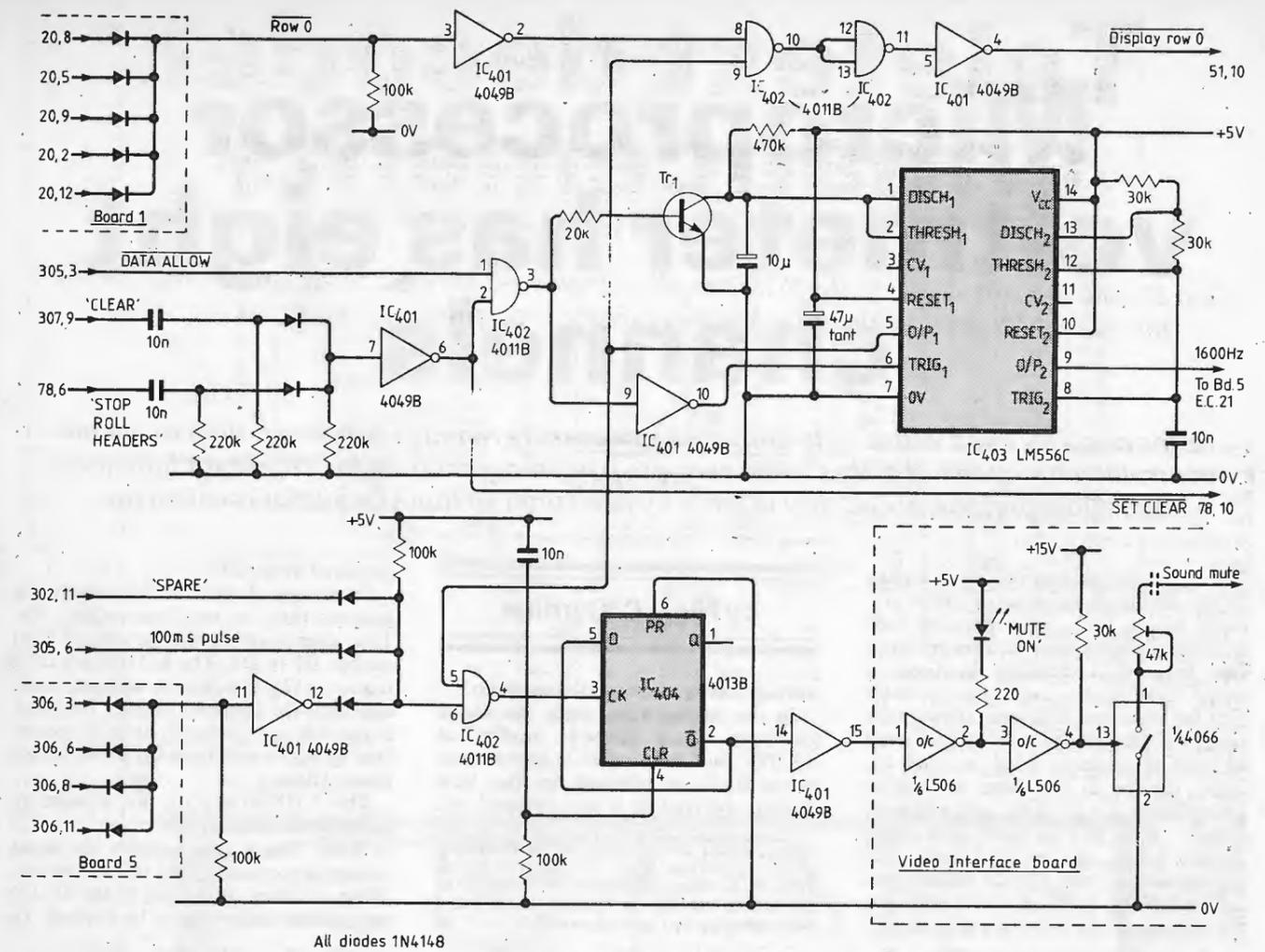


Fig. 2. On the same board as Fig. 1., these additions enable the viewing of the tv picture while the page is being selected; the generation of a clear-page pulse when the selected page is detected and the choice of a sound mute facility.

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source resistance ( $R_s$ ). One such graph is prepared for each measurement frequency, with  $v_T$  being calculated from the measured values of  $v_n$  and  $i_n$  using (1). Immediate comparisons are possible if the results from several devices are plotted on the same graph.

Reproduced below is a selection of graphs covering 1Hz to 10kHz, and comparing the following op-amps: 741, "Industry standard" bipolar input type. 3140, fet-input type. Very low current noise but poor voltage noise. OP-07, low-noise bipolar type. OP-37, ultra-low voltage noise, but poor current noise.

Using the graphs readily allows the best device to be chosen for a particular application (all other considerations being equal), or to see what trade-offs result from using alternative devices.

## Specimen graphs

At low frequencies, the OP-37 has the lowest noise (approximately 10nV/√Hz) for source resistances up to a few kilohms.

Above this, the OP-07 is best until around 100 kilohms, when the 741 almost matches its performance. For  $R_s$  greater than 1Megohm, the 3140 fet-input comes into its own, contributing the lowest noise (~800nV/√Hz).

There is less difference between the various devices at frequencies of 1kHz and above. The OP-37 still provides the best performance for  $R_s$  up to 20kΩ, after which the OP-07 and 741 are about equally good up to  $R_s=200kΩ$ . For source resistance greater than a few hundred kilohms, the 3140 once again becomes the best device, adding little significant noise to the thermal noise of the source itself.

At 10kHz, the OP-37 is still the lowest noise op-amp studied for  $R_s$  less than 20kΩ. The other three devices are all comparable for  $R_s$  up to 200kΩ, above which the fet-input of the 3140 once again provides the best performance.

For applications requiring low source resistances, say less than 10kΩ, the OP-37 can be used to advantage. For source resistances higher than a few 100kΩ, the 3140 has the best noise characteristic because of its fet input. Overall, the 741 performs

very well, being almost as good as the OP-07 "low-noise" op-amp except at low frequencies.

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# Assembly language programming

Before writing assembly-language programs one must understand microprocessor instructions; but only a few of these need be learnt to start programming, as Bob Coates illustrates in his third tutorial.

by R. F. Coates

This section looks at 6805 microprocessor instructions and how they are represented. Each assembly-language instruction consists of an operation-code mnemonic, of which there are 61, which produces one machine-code byte when assembled. The instruction indicates the addressing mode to be used (which modifies the op-code byte) and may also require an operand giving either data or an address.

A one or two-byte data or address in the operand is added to the op-code to complete the instruction hence each assembled instruction will be between one and three bytes long. To be able to program in assembly language one has to learn how to use the various instructions and this is best done by trying them out in small programs on the Picotutor and seeing how the operations modify data. But it is not essential that you become familiar with every instruction before starting out; programs can be written using a small proportion of the instructions. Some instructions are used more than others, and some hardly at all. Emphasis here is placed on the most commonly used instructions; instruction tables published in the April issue of *Wireless World* or by Motorola in the MC68705P3 data sheet and MC68705P3(AC1) reference card are needed. Instruction functions fall into one of five categories.

register/memory read/modify/write control  
branch  
bit manipulation

## Register/memory instructions

Instructions used in our previous example, LDA, STA, ADD and JMP, all fall into this category. With the exception of store and jump-type instructions, six different addressing modes can be used with each instruction mnemonic. The load accumulator instruction LDA is used here to demonstrate addressing modes; the principles are the same for all the other instructions.

Each addressing mode in the table has three columns indicating the op-code, which is machine code of the instruction mnemonic for the addressing mode specified, the number of bytes required (one for the op-code, any others for the

operand) and the number of microprocessor clock cycles required to carry out the instruction. The six versions of LDA are as follows.

**Immediate.** Here the accumulator is loaded with a specified data byte which will follow the op-code byte in the machine-code instruction. This is written in assembly language as LDA # $\$F$ , the hash sign in the operand field indicating immediate addressing mode and the dollar sign indicating that the data byte 2F is hexadecimal. When assembled the instruction reads

A62F LDA # $\$2F$

After the instruction is carried out the accumulator will contain 2F. With the addition of a software interrupt instruction, SWI, this program can be tried out on the Picotutor (use addresses between 24 and 6F).

A62F LDA # $\$2F$   
83 SWI

The interrupt instruction SWI passes control back to the monitor when the program run is completed in the same way as the JMP 80 instruction used earlier but it also places the contents of the processor A and X registers, condition codes and the address of the instruction following SWI in a temporary store called the stack. This information may then be retrieved and displayed on the Picotutor using the register function (reg) which is especially useful for program debugging since SWI interrupts may be placed anywhere in the program allowing the register status to be examined at each point.

Pressing the register key after such a break has passed control back to the monitor will display the condition codes as five bits (H, I, N, Z and C). If the letter is displayed the bit is set (1); if a dash is displayed on the bottom line the bit is clear (0). Pressing the step-up key will now result in the accumulator being displayed and pressing it again will display the index

register indicated by letter H. Another step up will show the three-digit program counter value indicating the address of the instruction following the SWI interrupt which caused the break. A final step up returns the stack-pointer position which indicates the position before the interrupt was encountered\*. This is because the stack pointer is moved down when the SWI interrupt stacks the c.p.u. registers. Pressing any key will return the dash prompt.

**Direct.** This version of the LDA instruction loads the accumulator with the contents of a memory location between 000 and 0FF as in

B680 LDA  $\$80$

In this example the accumulator is loaded with the contents of address 80. Again two bytes are required, one for the op-code and one for the two hexadecimal digits of the page-zero address. The absence of a hash symbol or X in the operand field indicates that direct (or extended) addressing is to be used. Try running this instruction followed by SWI on the Picotutor, and the accumulator should be loaded with CC which is part of the eeprom monitor program.

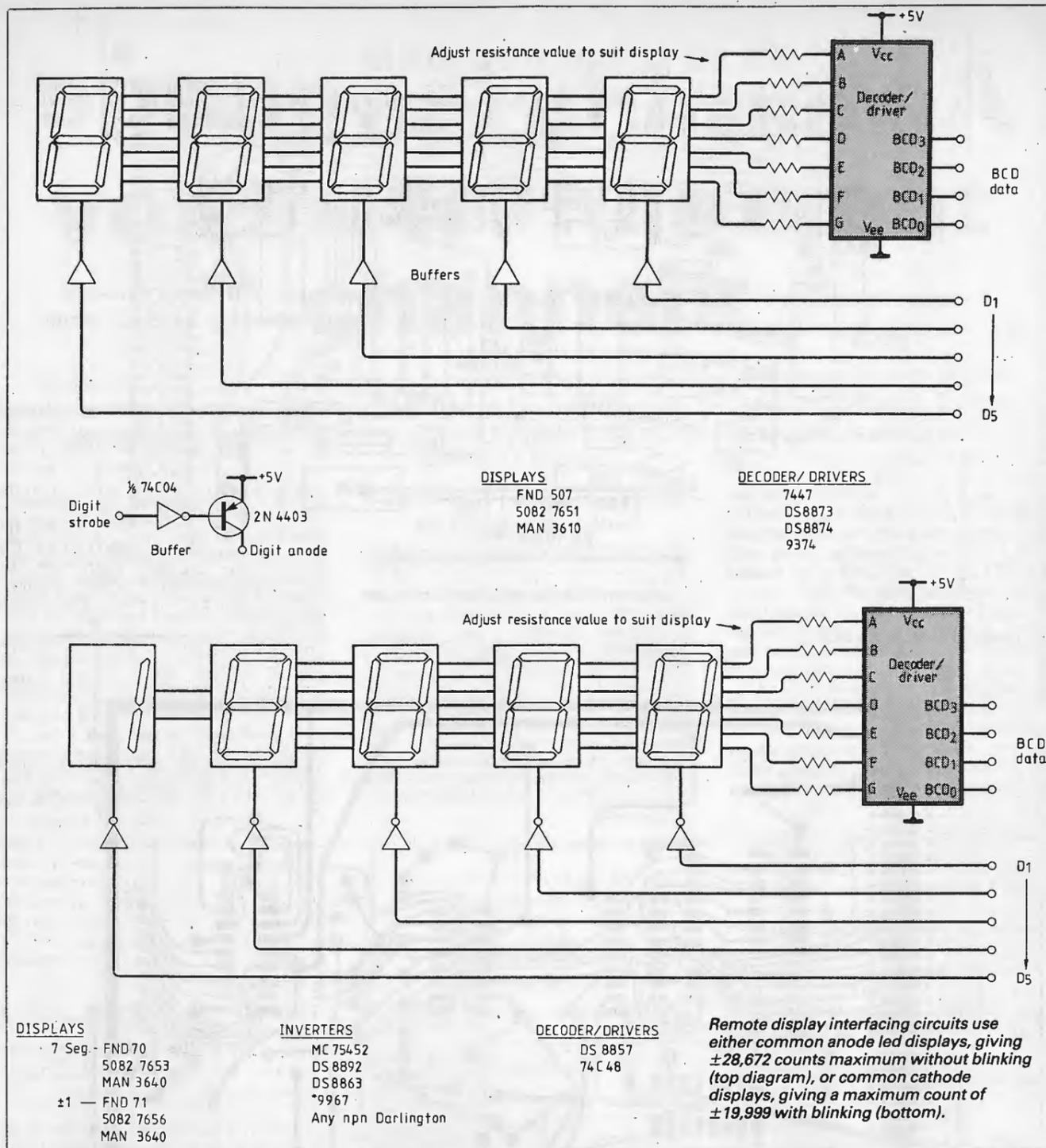
**Extended.** This is similar to direct addressing except that two address bytes are required to allow access to any location in the full memory map of 000 to 7FF, e.g.

C60080 LDA  $\$80$

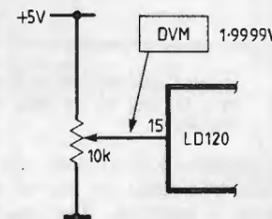
is the same instruction as in the direct-mode example above. As extended-mode addressing expects two bytes following the op-code byte, the full address must be specified. The assembly-language mnemonic and address are written in the same way for both direct and extended modes.

A computer assembler will look at the source code instruction to see first if direct addressing can be used. If it cannot, i.e. the address is above 0FF, extended-mode addressing will be used. The same principle applies when assembling by hand.

\*If Picotutor does not display the stack pointer but returns the dash prompt after the program counter you have an early version of the software which only displays registers if SWI is not placed in a subroutine.



shorting link removed and the circuit as shown below, adjust the voltage on pin 15 to as close to 1.9999V as possible (the loan of a d.v.m. will help here) and adjust the 10k $\Omega$  preset to give the same reading on the remote display. If there is access to a scope, check the clock frequency, which should be approximately 163kHz, and also the waveforms on pin 6 of IC<sub>5</sub> and pin 16 of IC<sub>3</sub>, should be as shown.



The d.v.m. board is now ready for interfacing to the Z8.

The appropriate Basic program can now be entered with the machine-code program, which when run will display the

voltage appearing on the selected input if outside the preset values.

## Applications

The application shown here uses the d.v.m. board to monitor eight channels, each given a fixed minimum and maximum in the program. This could be modified to allow the user to input the values when the program is executed. When a reading falls out of range, the minimum and maximum values are displayed on the terminal. An additional program for dialling up on a telephone line when the minimum and maximum values are exceeded could be incorporated, to send an alarm message to a host computer.

continued on page 58

# Forth computer

With applications ranging from video games to research and process control this microcomputer combines the powers of Forth, a fast, threaded computer language/operating system, with an eight-bit processor having 16 bit internal architecture.

**Table 1. A program for adding two 16bit numbers on the Picotutor using assembly-language mnemonics devised for the 6805 microprocessor.**

030	B651	LDA	\$51	Add least sig. bytes of the 2 numbers, result in 55.
032	BB53	ADD	\$53	
034	B755	STA	\$55	
036	B650	LDA	\$50	Add most sig. bytes of the 2 numbers and carry from addition of least sig., result in 54.
038	B952	ADC	\$52	
03A	B754	STA	\$54	
03C	83	SWI		Return to monitor.

**Table 2. Program for subtracting two 16bit numbers using 6805 mnemonics may be expanded to subtract numbers of any length in multiples of eight bits.**

030	B651	LDA	\$51	Subtract least sig. bytes of the 2 numbers, result in 55.
032	B053	SUB	\$53	
034	B755	STA	\$55	
036	B650	LDA	\$50	Subtract most sig. bytes of the 2 numbers and borrow from 1st operation, result in 54.
038	B252	SBC	\$52	
03A	B754	STA	\$54	
03C	83	SWI		Return to monitor.

Use direct mode wherever possible because it uses one less byte of memory space. In the previous example direct mode would be used although extended mode would work but with this example extended mode must be used

C607FE \$7FE

Try running this (followed by SWI) and it will load the accumulator with 02, again part of the monitor program.

Three remaining addressing modes are all indexed types so to demonstrate their use with LDA we must first load the index register, X, using LDX. This operates in exactly the same way as LDA so

AE80 LDX #\$80

will load the index register with 80. The operand for indexed addressing modes is written as (offset),X where 'X' indicates indexed addressing; which of the three variants is used is determined by the size of the offset. If no offset is required this assembles as

F6 LDA 0,X

Indexed, no-offset mode requires only the op-code byte, the effective address of the data or argument being held in the 8bit index register. This mode gives access to the first 256 memory locations from 000 to 0FF. It is often used to move a pointer through a table or to hold the address of a frequently used i/o location. Run this example,

AE80 LDX #\$80  
F6 LDA 0,X  
83 SWI

and then examine the registers. Index register X should contain 80 and the accumulator CC, the contents of memory location 80.

In the indexed, 8bit-offset mode the effective address is the sum of the contents of the index register and the offset byte following the op-code. This allows access to the first 511 memory locations from 000 to 0FE and two bytes are required for each instruction, e.g.

E601 LDA 1,X

The offset may be specified in the operand field as a decimal (1 to 255) or in hexadecimal (01 to FF). A computer assembler

automatically converts decimal numbers to hexadecimal hence either of the following may be used

E6FF LDA 255,X  
or E6FF LDA \$FF,X

Try this example.

AE00 LDX #0  
E680 LDA \$80,X  
83 SWI

It should give the same results as the previous example.

The indexed, 16bit-offset mode operates in a similar way to the 8bit-offset one but two extra bytes are required after the op-code to contain the 16bit offset, making three-bytes. A 16bit offset allows access to any location in the memory, e.g.

AE85 LDX #\$85  
D60700 LDA \$700,X  
83 SWI

should load the accumulator with AE, the contents of memory location 700+85 or 785 which is in the mask-programmed rom of the 68705P3 (programmed by the manufacturer).

Which of the three indexed modes to be used is not indicated directly in the assembly-language source code; which is used is determined by the offset size. A computer assembler will choose the mode which requires the least number of bytes and this applies when assembling by hand. The main use of the two indexed-with-offset addressing modes is when scanning tables of data in memory. Normally the base address of the table is the value of the offset and initially, zero is loaded into the index register to point to the first value in the table. If the index register is incremented repeatedly, access can be gained to the successive values of tables up to 256byte long. This now covers the six addressing modes that can be used with LDA.

### Other instructions

The same basic principles apply to other instructions in section one of the instruction set, so for the other instructions we will just use one of the addressing modes to demonstrate their operation. LDX, the instruction for loading the index register, has already been covered.

**Store accumulator, STA.** This stores the

**Table 3. 16bit addition and subtraction programs for 6800/6809 microprocessors. By coincidence, machine code for direct addressing on the 6805 processor is the same as for extended addressing on the 6800/6809 types.**

16bit addition			
1030	B61051	LDA	\$1051
1033	BB1053	ADDA	\$1053
1036	B71055	STAA	\$1055
1039	B61050	LDA	\$1050
103C	B91052	ADCA	\$1052
103F	B71054	STAA	\$1054
1042	7E7D97	JMP	START

16bit subtraction			
1030	B61051	LDA	\$1051
1033	B01053	SUBA	\$1053
1036	B71055	STAA	\$1055
1039	B61050	LDA	\$1050
103C	B21052	SBCA	\$1052
103F	B71054	STAA	\$1054
1042	7E7D97	JMP	START

**Table 4. 16bit addition and subtraction programs written in assembly language for the Z80 microprocessor. Add and subtract instructions cannot operate on memory directly so the HL register pair is used as a pointer.**

16bit addition			
2000	215320	LD	HL,\$2053
2003	3A5120	LD	A,(\$2051)
2006	86	ADD	A,(HL)
2007	325520	LD	(\$2055),A
200A	2B	DEC	HL
200B	3A5020	LD	A,(\$2050)
200E	8E	ADC	A,(HL)
200F	325420	LD	(\$2054),A
2012	C30000	JP	START

16bit subtraction			
2000	215320	LD	HL,\$2053
2003	3A5120	LD	A,(\$2051)
2006	96	SUB	(HL)
2007	325520	LD	(\$2055),A
200A	2B	DEC	HL
200B	3A5020	LD	A,(\$2050)
200E	9E	SBC	A,(HL)
200F	325420	LD	(\$2054),A
2012	C30000	JMP	START

contents of the accumulator in a memory location dictated by the addressing mode used, e.g.

AE40 LDX #\$40  
E707 STA \$7,X

will store the accumulator contents in address location 40+7. The only exception is that immediate addressing cannot be used as this would imply storing in the byte following the op-code which is part of the program.

**Store index register, STX.** Identical to STA but used for the index register.

**Add memory to accumulator, ADD.** Contents of the accumulator are added to a memory location (or an immediate byte) according to the addressing mode, placing the result in the accumulator. If the result is greater than 8bit the carry bit (C) in the condition-code register (CCR) is set, if not the bit is cleared.

Continuing the instruction-set description, the next article covers logical functions, leading to the next group - read/modify/write instructions.

Today a home or personal computer can more than match at lower cost the performance of a typical mid-1970s minicomputer. Then a minicomputer costing tens of thousands of pounds would have a memory of less than 32K words with a cycle time of about a microsecond and a Teletype terminal capable of ten characters per second. Disc-drive memory was rare and expensive and double-precision/float-point instructions would be executed by software. This microcomputer design costing a few hundred pounds has a 48K read/write memory operating at 666ns, further 8Kbyte rom containing the operating system, a 100-character-per-second terminal and a 200Kbyte disc memory.

	Forth computer	1970s minicomputer
Memory size	56K (48K ram, 8K rom)	64K ram
Memory speed	666ns	960ns
C.p.u. 16-bit add time	4.6µs	1.96µs
Output peripherals	composite video RS232 8 ports	64 ports
Input peripherals	parallel keyboard RS232 8 ports	standard peripherals
Disc storage	200Kbyte/drive	5Mbyte/drive
Access time	333ms	35ms
Cost	£100-500	£10,000-100,000

The cost of developing control software and language application packages is the main reason why low-cost microprocessors have not destroyed the minicomputer industry. It will be a long time before any microprocessor has the software support of the PDP11! Further, when designing a home computer from the i.cs upwards one does not have the support of other computers to develop the software on and one cannot afford to develop the software alone. For these reasons the control program was chosen from those already available. This also applied to the choice of language; I was not willing to start from the bottom with machine code, for one sees too little reward for the effort of keying in programs on a hexadecimal keypad, nor was I prepared to design a 'bootstrap' rom that loaded the operating system in from disc, for I felt it an unnecessary com-

mitment while the rest of the system was unproven.

### Language/operating-system choice

The most popular operating system and language in the microcomputer field are CP/M and Basic respectively. Although Basic is readily available, in for example the INS8298 rom for the 8080, I was not prepared to use the language for reasons too many to mention but summed up by Dijkstra<sup>1</sup> who said "It is practically impossible to teach good programming to students that have had prior exposure to Basic." He seems equally impressed by most other languages, including Fortran, PL/1, Cobol, APL and Ada.

My first choice would have been Pascal but for this application Forth appeared to be the best choice. Besides being a language, Forth forms the basis of an operat-

by Brian Woodroffe

ing system and the Forth Interest Group<sup>2</sup> have made FIG Forth a public-domain product. The language is efficient, which is important when using a processor with a limited address range of 64K and it is interactive, avoiding the traps of edit-compile/load-run phases which are a left over of batch-processing systems. FIG Forth is a single-operator, single-task operating system but it has 'hooks' which allow it to be expanded into a multi-operator, multi-task system. It promotes good programming habits in that its programs are structured in blocks and work from top to bottom.

The language has drawbacks - unfamiliar notation, no file structure and poor data structures - but it is readily available and has more advantages than disadvantages. The power and flexibility in Forth allows the operator to expand the language and add any desired feature, and a new version of Forth may be placed on disc by editing and compiled using the resident language to give a completely user-defined version.

### Forth

Details of Forth and how it operates are available (ref. 3) and the following is a brief summary. Forth uses 16bit arithmetic and reverse Polish notation, which implies the use of a data stack. Control between executable statements, referred to

as a word, is accomplished by the use of indirect-threaded code and a control stack which is separate from the data stack. Features of Forth not found in Basic are virtual memory, compiling, extensibility and vocabularies. These features make better use of the processor resources and a program written in Forth will use less memory and run faster than its Basic equivalent, often by a factor of ten or more in both cases. As Forth compiles the 'English' program into a form readable by the processor (threaded code) the operating speed will always be faster than when using Basic which stores the program as text. Memory space taken up by compiled code is much smaller than would be taken up by its equivalent in English text so larger programs are possible in a limited memory space.

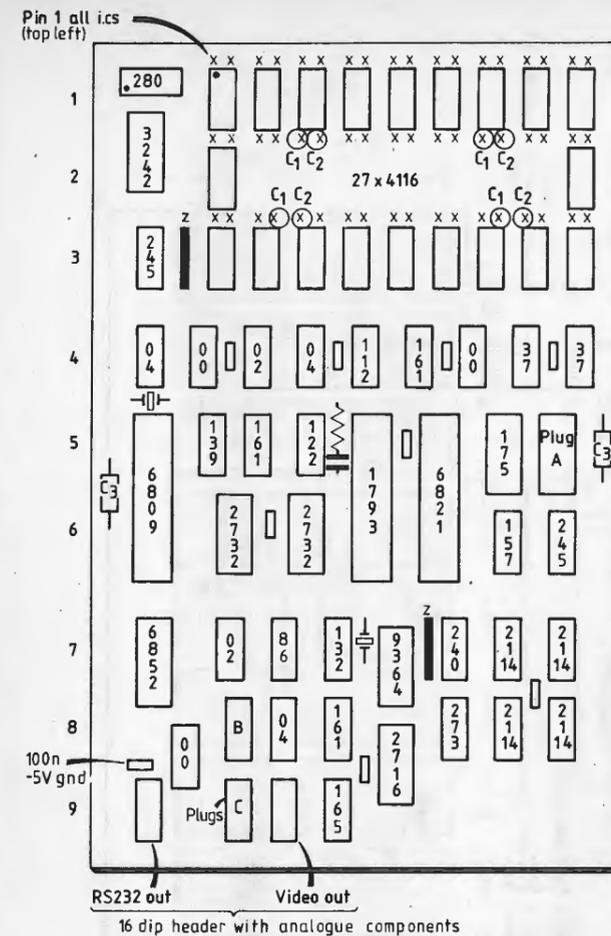
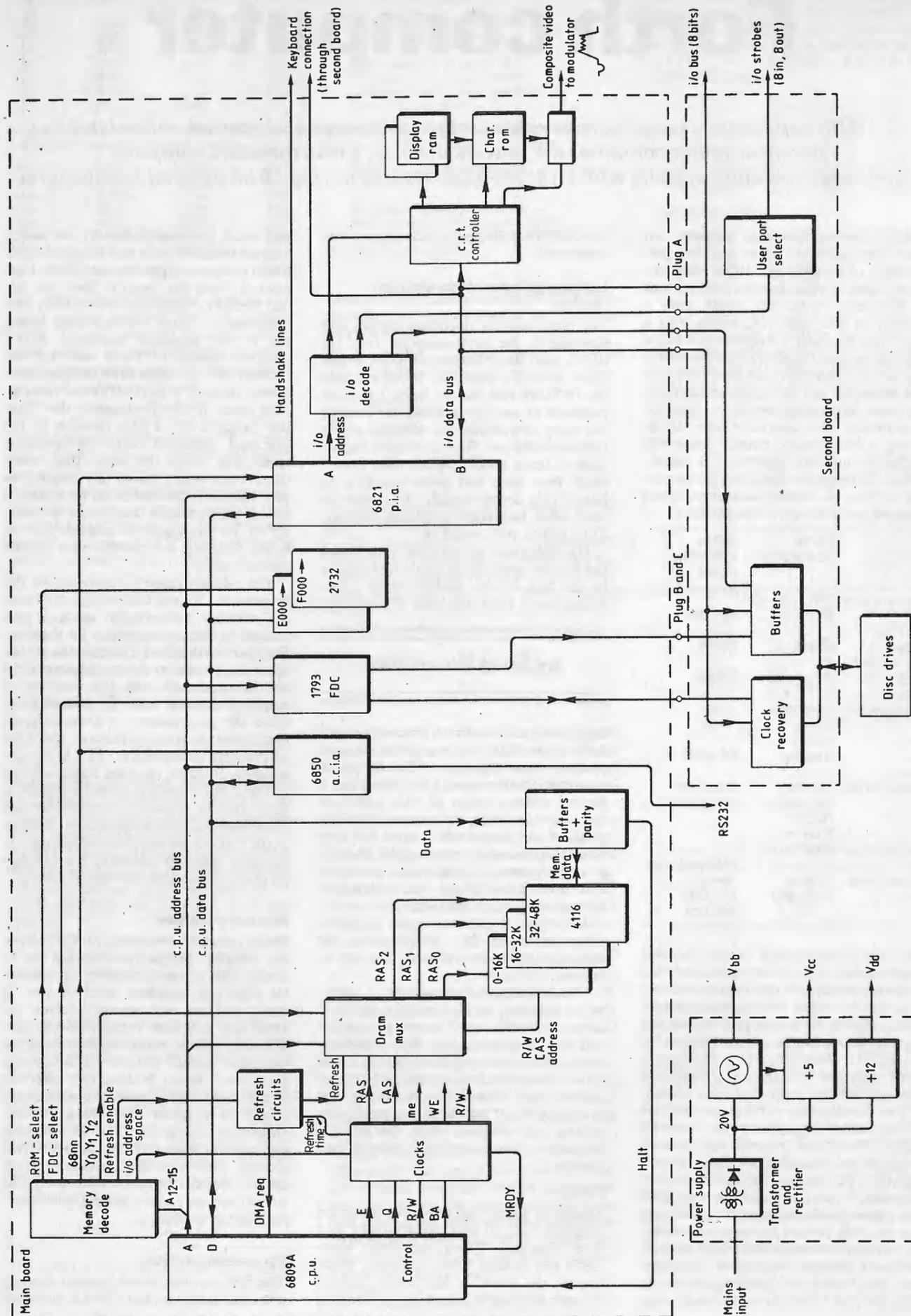
The virtual-memory feature allows the programmer to treat disc storage as processor memory so memory space is not limited by the processor but by the disc. Data is moved to and from the disc by the operating system so the programmer need not be concerned with the problem of mapping the disc memory. Vocabularies allow the programmer to keep different application programs in memory which are physically concurrent but logically separate. Further, there are features found in Forth that are not generally available in Basic such as recursion, extensibility and self-compiling. Recursion allows a portion of the code to use itself more than once at the same time and extensibility is the ability of Forth to define new control words.

### Memory choice

Before selecting a processor for the computer, another design decision has to be made. This concerns memory, in particular what type and how much to use. In time, memory will always become too small and too slow because of the programmer's rising expectations of what the computer should do<sup>4</sup>, so 4116 dynamic rams were chosen because they offer the best performance in terms of cost, size and power consumption when compared with static rams such as the 2114. This decision does present some problems in that refresh circuits and three-rail supplies are required. Because dynamic rams are prone to 'soft' errors, parity-checking circuits are included in the design.

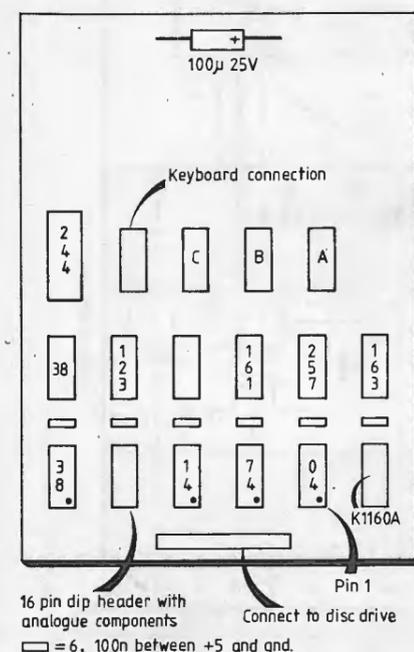
### Processor choice

The Z80 microprocessor contains dynamic ram refresh circuits and CP/M is written in



- C1 10μ 25V Al +12V supply (4 places)
- C2 10μ 25V Al -5V supply (4 places)
- C3 100μ 25V Al +5V supply (2 places)
- C4 100n between +5V/gnd (8 places)
- x x 100n between +12V/gnd and 100n between -5V/gnd (in 27 places)
- z Single in line 10k pullups (in 2 places)

ics are numbered as follows, IC43 means 4th row down 3rd one in i.e. IC43 is an LS02



Complete Forth computer system has a 48K memory, floppy disc storage and memory-data parity checking but the system may be used with 16K ram and without disc storage and parity checking to reduce costs. Wire wrapping allows the computer to be built on one relatively small board with a minimum of bus buffering. A further small board holds the disc controller and i/o-port hardware. The system can be set to read most disc formats.

Z80 machine code which surely explains why it is the most widely sold processor, but to use Forth, the most suitable 8bit microprocessor is the 6809. Although most of Forth is written in Forth, the computer must execute some machine code to interpret the most primitive Forth instructions. The 6809 has indexed addressing modes (see "6809 evaluation system" by R. Coates, *Wireless World* July 1980) which suit stack operations and as said earlier, Forth uses two stacks. These examples of stack addition illustrate the merits of the 6809; they represent code of the Forth word '+' for various processors.

6809	Z80/8085	6800
PULU	D POP	D PULB
ADD 0,U	POP H	PULA
STD 0,U	DAD H	TSX
	PUSH H	ADDB 1,X
		ADCA 0,X
		STB 1,X
		STA 0,X

6502	8088	6502
CLC	POP AX	JMP NEXT
LDA 0,X	POP BX	LDY #1
ADC 2,X	POP BX	LDY [IP],Y
STA 2,X	ADD AX,BX	MOV DX,BX
LDA 1,X	PUSH AX	MOV DX,BX
ADC 3,X		INC DX
STA 3,X		DEY
INX		ADCA #2
INX		STA IP

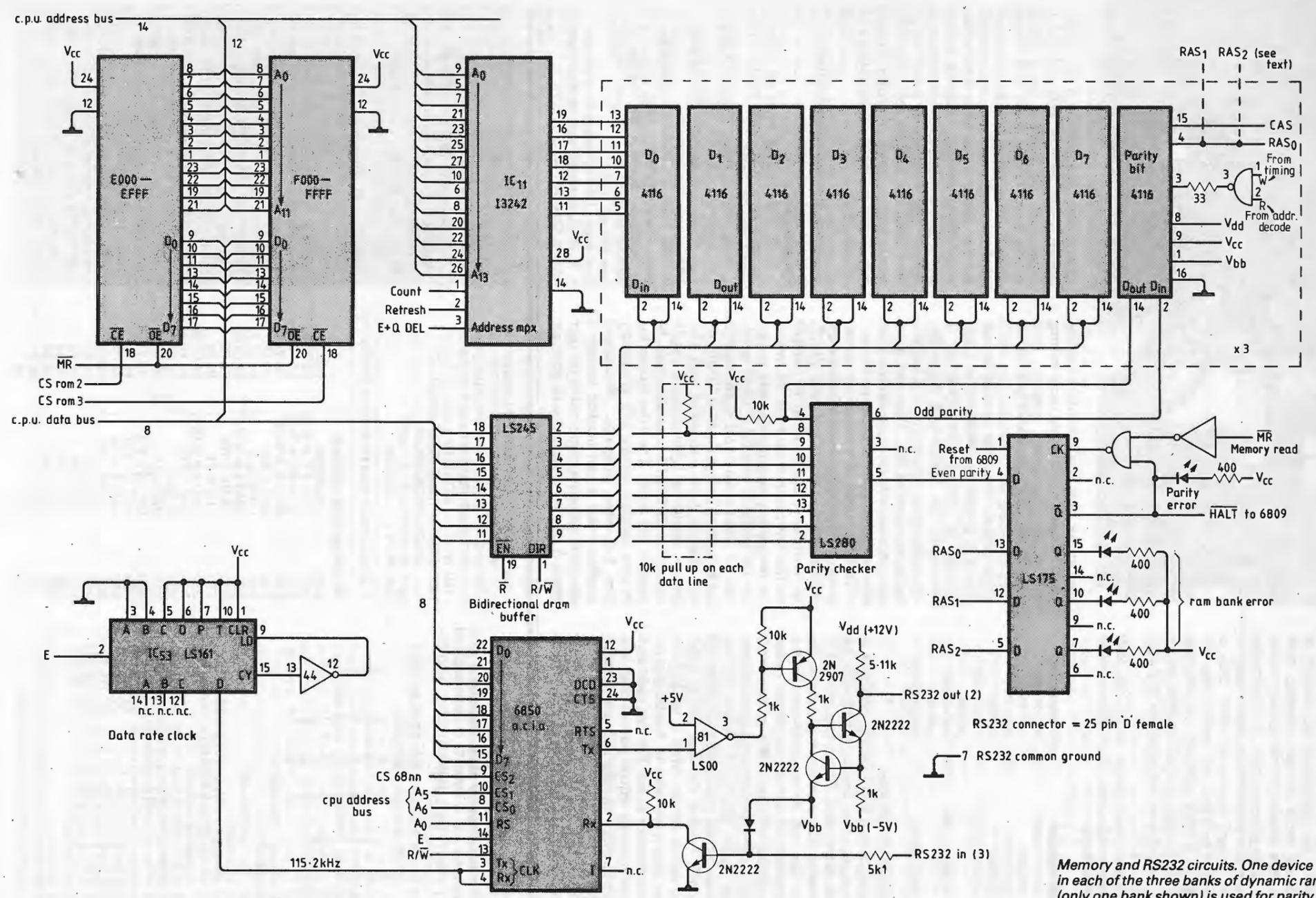
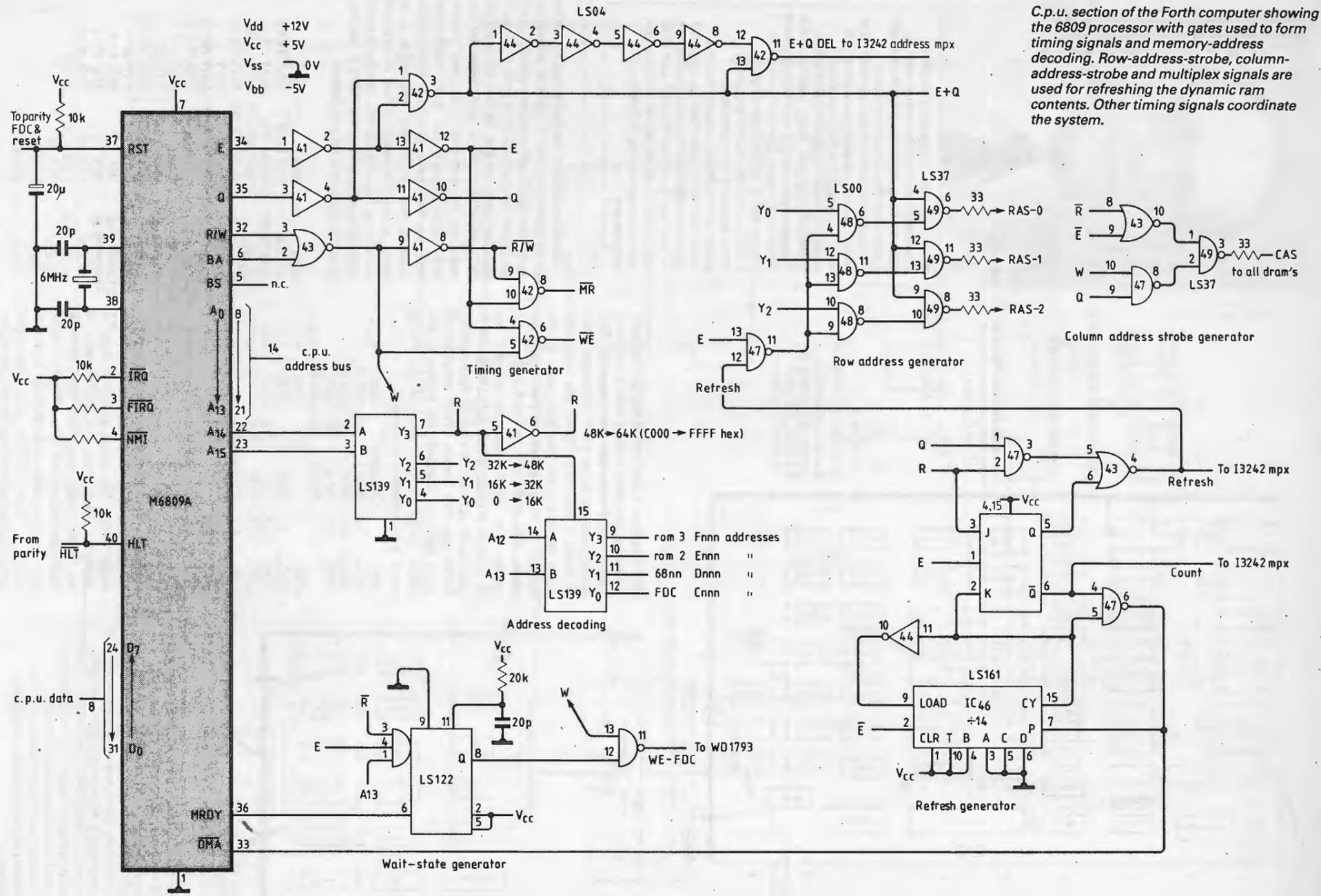
Secondly, the 6809 instruction set is particularly suited to code the crucial Forth word 'next'. The speed at which 'next' is executed determines the performance of the Forth system since this word controls the indirect-threaded code. 'Next' is called the inner (or address) interpreter to distinguish it from Forth's text interpreter which performs the function of a compiler.



Having worked in Hewlett Packard's production and systems-engineering departments, Brian Woodroffe currently works with the company's South Queensferry research and development group and has recently been involved with designing the microprocessor control section of the HP3724/25/26A baseband analyser. Brian obtained a BA degree in engineering and economics at Downing College, Cambridge in 1970 and an MA in 1975. His computing interests include real-time control, languages and microprocessor graphics but outside electronics, his main interest - rifle shooting, in which he has represented Scotland in full bore - has been curtailed through part-time studies for an M.Sc degree in computer systems engineering at Edinburgh University.

Machine code in the computer emulates Forth operation, the Y register taking on the role of the Forth program counter, and the Forth instruction-fetch cycle is a 'next' machine-code routine. So you can see that the processor choice is dominated by the speed and memory cost of the 'next' operation. Equivalent Forth 'next' operations for some microprocessors are listed below. Because the 6809 'next' operation is so short, it may be copied in line as required resulting in improved performance through avoiding the JMP NEXT instruction required for most processors.

6809	8088	6502
LDX 0,Y++	JMP NEXT	JMP NEXT
JMP [0,X] (4.11)	LODS AX	LDY #1
	MOV BX,AX	LDY [IP],Y
	MOV DX,BX	STA W+1
	INC DX	DEY
Z80/8085	JMP WORD	LDY (IP),Y
JMP NEXT	PTR (BX)	STA W
LDAX B		CLC
INX B		LDY IP
MOV L,A		ADC #2
LDAX B	JMP NEXT	STA IP
INX B	LDX IP	BCC \$+4
MOV H,A	INX	INC IP+1
MOV E,M	INX	JMP W-1 (1.25)
INX H	STX IP	
MOV D,M	LDX 0,X	
XCHL	STX W	
PCHL	LDX 0,X	
(1.37)	JMP 0,X	
	(1)	



Values in parentheses are merit figures obtained by multiplying the number of processor cycles by the processor cycle time then dividing by the memory-access time in the processor cycle. It is interesting to note that the 6809 fares better than the more recently introduced 8088. This is especially so when one realises that the 8088 has a 16bit arithmetic unit whereas the 6809 in common with the other processors noted has an 8bit arithmetic and logic unit (a.l.u.).

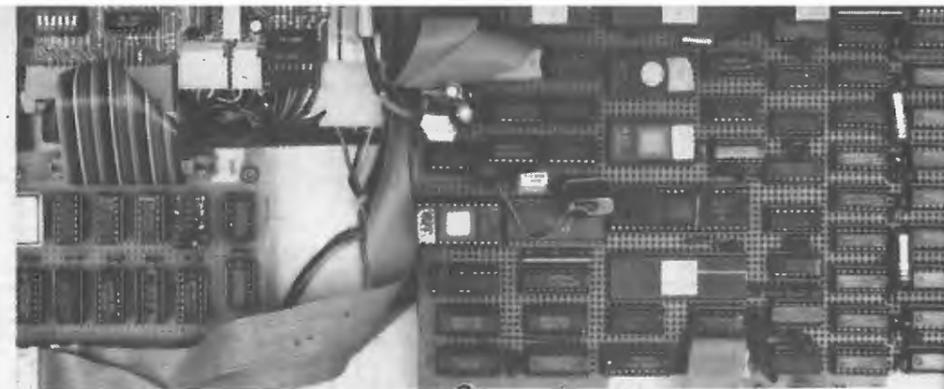
Finally, the register set of the 6809 exactly matches that which is required to operate Forth.

6809 register	Forth operation
S system stack pointer	RP return stack pointer
U user stack pointer	SP data stack pointer
Y index register	IP instruction pointer
X index register	W code field pointer
D accumulator	accumulator

### Peripheral devices

Having chosen Forth and the processor to run it on, other design requirements are easily determined. These were selected to maximize the number of peripheral devices that can be easily driven. First a floppy disc was included to provide a modest amount of non-volatile memory with much faster operation than tape recorders. Mini floppy discs were chosen for two reasons, firstly because they are cheap and secondly because the data rate of eight-inch double-density drives is too high for most microprocessors to handle without direct-memory access. Further, eight-inch drives normally require phase-locked loop clock-recovery circuits and also a mains supply.

Three-inch disc drives from Sony were investigated but the data transfer rate is



high so that only single-density recording could be used, which would mean wasting half of the data-storage capacity. Both these drives and eight-inch types can be used with the system, provided they run in single density. Processor memory in this system is greater than 40Kbyte so a disc capacity of greater than 400Kbyte is reasonable; one double-sided floppy-disc drive meets this requirement. It is interesting to note that the BBC Micro and Atom computer can only use single-density 5 1/4 inch disc drives because of data-rate problems.

Different types of terminal are accommodated. Operating-system words for terminals, KEY, TERMINAL and EMIT, are vectored so that they may be changed on-line between terminal types. At switch-on the system automatically sets vectors for the available terminals. These terminals are either serial RS232 or 8bit parallel for a keyboard such as the RCA VP601/611 and integral video compatible with 625-line tv, displaying 1,024 characters in 16 lines (the EF96364B controller may be used for 525 lines). The video section has its own memory, leaving 48K of memory free for other programs. Bit-mapped graphics video is best handled through a secondary processor connected to the user ports. A number of definable i/o ports are

spare to allow for expansion of the system. Certain design features were included to reduce cost. By keeping the computer system down to one board, bus drivers necessary to overcome capacitance encountered in larger systems are avoided. Another reason for avoiding these buffers is that they cause delays which eat into the access time available from communicating devices. The switch-mode power supply used means that a readily obtainable transformer with a single secondary winding may be used to provide all three rails (+12, +5 and -5V).

Next article describes computer circuitry.

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# LETTERS

## CABLE AND AMATEURS

As our very good friend Pat Hawker (G3VA) has mentioned on more than one occasion the question of cable tv (c.a.t.v.) being installed for tv links and its possible QRM (interference) to the amateur bands between 5MHz and possible infinity (GHz?) is looming.

With the notification of the RFI Bill 5.929 last September, it would appear that 'we' as the amateur population are dragging our feet somewhat.

Hopefully, as I ask you to publish these few words, someone somewhere, here in the UK at least, will take note to realise that if c.a.t.v. is to progress without (?) problems then parties must get together quickly.

It not only affects the amateur and/or industry-at-large but in some cases the s.w.l. and domestic listener/viewer.

Bear in mind that radio amateurs throughout the world form a substantial part of the balance of payments of varying countries, and after all, not every firm depends on MOD contracts. The naive idea that amateurs 'do not count' according to some professional engineers must be looked at in the light of future and past developments in both radio and tv. In short, what works in theory doesn't always work in practice, so consequently the need for liaison between interested parties, notably the RSGB on the one hand and industry and the Home Office on the other. The RSGB and others are aware of this problem regarding c.a.t.v. and it should not be allowed to drift.

J. A. Holmes, G4LRS  
Chingford  
London

circuit is shown below; it is a standard high-power current sink set at one amp. per volt of  $V_{ref}$ , and gated by the pulse train to pin 8. One circuit is required for each phase of the motor which in this case is a large V.R. type.

This circuit has been in use since early 1977; I had no reason to suppose it was novel then.

B. S. Beddoe  
Wimborne  
Dorset

## HERETICAL PHYSICS

Those of us who are approaching the age of 80 can hardly bear to wait a month to find out what kind of Newer Physics is going to turn up in the *WW* "Letters". Some of the ideas are so oddly fascinating that it seems a real pity that they cannot all be right.

Attractive though this is, I cannot help remembering the professor of physics who reminded his students that what happened on the lab. bench was real, whereas what went on inside human heads was mostly fantasy, and often pathological fantasy at that.

P. C. Smethurst,  
Bishop's Stortford, Herts.

## ELECTROMAGNETIC DOPPLER

In your March 1983 issue, your correspondent J. Kennaugh asks how the Doppler shift is produced in electromagnetic waves. Specifically he quotes the relativistic Doppler equation as:

$$\frac{f_o}{f_s} = \left(\frac{c-v}{c}\right) \left(\frac{1}{\sqrt{1-v^2/c^2}}\right)$$

and asks "what is the physical mechanism which produces the first term?". The "physical mechanism" is the velocity,  $v$ .

J. K says that if the wave propagation velocity is the same to both observers then the only possible variable is time. I don't understand why J.K. says this. If two objects are travelling away from each other then the distance between them is increasing.

If one of these objects generates something - say "wave crests" - at regular intervals, and if

these wave crests travel through space to the other object, then each successive crest has further to travel and consequently takes longer over the journey. The frequency of arrival is lower than the frequency of departure. If we take the transmission frequency to be  $f_s$  and the received frequency to be  $f_o$ , the relative velocity between the objects as  $v$  and the propagation velocity as  $c$ , then for "modest"  $v$  a moment's work with pencil and paper gives:

$$\frac{f_o}{f_s} = \frac{c-v}{c}$$

In this equation  $f_o$ ,  $f_s$ ,  $c$  and  $v$  are all measured by the same observer. J.K. says that  $(c-v)$  is the velocity of light relative to the observer. Not true.  $(c-v)$  is the difference between the rate at which light (or radio waves) cross the gap ( $c$ ) and the rate at which the gap is increasing ( $v$ ).

Note that this last equation arises naturally from the definitions of velocity and frequency - no obscure "physical mechanism" is needed.

Another point. If both objects transmit at identical transmitter frequency then each will receive a lower frequency (Doppler shifted) than they transmit. At object A, the transmitter frequency  $f_A$  is higher than the received frequency from B ( $f_B$ ) -  $f_A > f_B$ ; at B, by the same process  $f_B > f_A$ . There is a sense in which  $f_A > f_B$  and  $f_A < f_B$ . If you think that this "doesn't conform to the laws of mathematics" then you have three (not two) choices: reject the Doppler effect; reject maths; or find an error in your "deduction".

S. Hobson  
Hampton  
Middlesex

I have been unable to find the answer to what is superficially a straightforward question: what is the mechanism by which Doppler shift is produced in the case of electromagnetic waves?

In acoustics, when two observers in relative motion observe the same sound wave they measure different frequencies because the wave is passing each at a different relative velocity. If  $V_{R1}$  and  $V_{R2}$  represent the velocities of observers 1 and 2 relative to the wave then

$$f_1 \lambda = f_2 \lambda \quad (1)$$

$$\text{or } \frac{f_1 - V_{R1}}{f_2 - V_{R2}} = \frac{V - v_1}{V - v_2} \quad (2)$$

Equation (2) is the derivation of the more familiar form of the equation where the relative velocity of wave and observer is expressed in terms of the velocity of propagation in the medium  $V$ , and the velocity of the observers relative to the medium  $V_1$  and  $V_2$ .

The e.m. Doppler shift equation (3) can be verified experimentally to a high degree of accuracy.

$$\frac{f_o}{f_s} = \frac{c-v}{c} \quad (3)$$

Now if, as I have seen stated, "similar principles apply" one can deduce two things.

- (1) that the velocity of light relative to the observer is  $c-v$ , which is in direct opposition to the postulate of relativity which insists that the velocity of light is always  $c$  independent of relative motion between source and observer;
- (2) that the velocity of light is constant relative to the source, which would provide an ade-

continued from page 50

### Z8 Basic listing for eight-channel a to d converter (@ = byte, % = hexa-decimal)

```

1 PRINT "SILICONIX LD120/121A TO Z8
INTERFACE"
2 PRINT "HIT ANY KEY TO RUN": GO
@%61,%07:R=USR(%54)
5 A = { } : B = { }
10 C = { } : D = { }
15 E = { } : F = { }
20 G = { see* } : H = { see* }
25 I = { } : J = { }
30 K = { } : L = { }
35 M = { } : N = { }
40 O = { } : P = { }
45 IN = 1 : Z=%80
50 @2=Z
55 @3=%A0:03=00
60 @2=%00
70 W = W+1:IFW<15 THEN 70
80 W = 0:GO@%1400 (m.c. routine for
collection of data)
85 IF N=1 THEN X=A: Y=B: GO TO 130
90 IF N=2 THEN X=C: Y=D: GO TO 130
95 IF N=3 THEN X=E: Y=F: GO TO 130
100 IF N=4 THEN X=G: Y=H: GO TO 130
105 IF N=5 THEN X=I: Y=J: GO TO 130
110 IF N=6 THEN X=K: Y=L: GO TO 130
115 IF N=7 THEN X=M: Y=N: GO TO 130
120 IF N=8 THEN X=O: Y=P: GO TO 130
125 GO TO 45
130 Z=Z+%10
135 V=@%26+@%25*10+@%24*100
+@%23*1000+@%22*10000
410

```

```

140 IF V>X THEN PRINT "CHANNEL":
N;"OVERRANGE":GO TO 1000
145 IF V<Y THEN PRINT "CHANNEL":
N;"UNDERRANGE":GO TO 1000
150 N=N+1:GO TO 50
1000 GO@%61,%07:PRINT @%22:"";
@%24:@%25:@%26;
1010 PRINT"MAX";X;"MIN";Y
1020 N=N+1:GOTO50

```

\*Limits entered here for process monitoring.

### Machine code routine

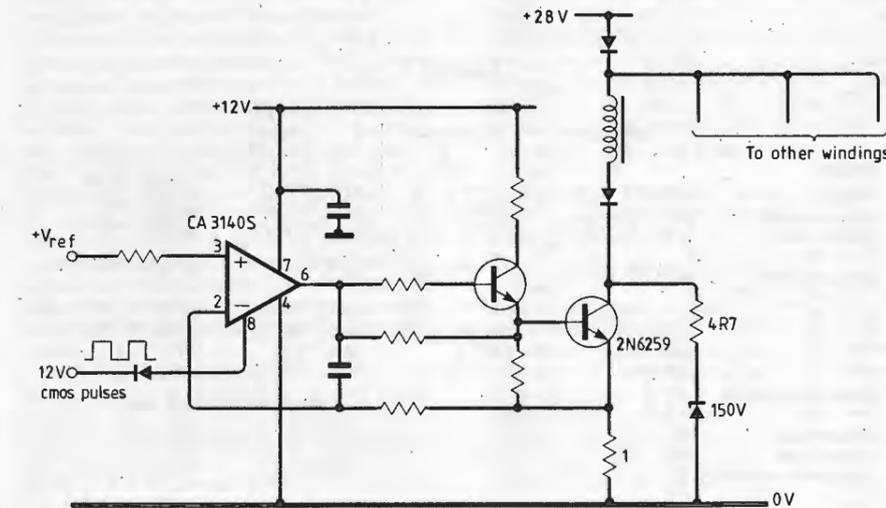
Line	Assembler	Hex
200	LD % F7, # % 41	E6 F7 41
210	LD % F6, # % 0F	E6 F7 0F
220	AND 3, # % 04	56 03 04
230	JRZ, * 220	6B FB
240	LD % 22, 2	E4 02 22
250	AND 3 # % 04	56 03 04
260	JR N2, * 250	EB FB
270	CLR % 21	B0 21
280	AND 3 # % 08	56 03 08
290	JRZ, * 270	6B FB
300	PUSH 2	70 02
310	INC % 21	20 21
320	CP % 21, # 4	A6 21 04
330	JRZ 2, * 350	6B 07
340	AND 3, # 08	56 03 08
350	JR N2 * 320	EB FB
360	JR * 270	8B EB
370	POP % 26	50 26
380	POP % 25	50 25
390	POP % 24	50 24
400	POP % 23	50 23
410	RET	AF

### Using the Z8 microprocessor

The potential of the Zilog Z8 microcomputer for low-volume or one-off applications has not been well publicised. Introduced in 1981, the chip includes all the blocks that you would find in a standard computer system including c.p.u., ram, i/o and a rom containing Tiny Basic. In addition there are two timers, one for serial i/o, the other available to the user. External memory of 60K can be added for program storage together with 60K of data storage. The evaluation kit used in this was supplied by Ambit International and possesses a comprehensive monitor, enabling machine-code routines to be written in Assembler and stored in eeprom. The Tiny Basic name does not reveal the full potential of itself, and with an 8MHz clock driving the Z8, it executes most of the instructions in 1.5 to 2.5  $\mu$ s.

## STEPPER MOTOR DRIVE

The 'Stepper motor driver circuit' article (*WW* February 1983) describes as novel a system which is certainly not new. A t.t.l. chopper drive circuit, while efficient, was found to cause excessive radiated interference (up to 400MHz) when fitted to an aircraft, so I designed a pulsed constant-current circuit using exactly the same principles as in Mr Bailey's article. A simplified



quate explanation of the null result of the Michelson-Morley experiment and would support the corpuscular/photon model of light, photons being "shot" out of matter at constant "muzzle" velocity.

A further piece of evidence supporting (2) is that of star aberration. In 1729 Bradley showed that the apparent direction of a star is actually the vector sum of velocity of the light from the star and that of the earth. It would seem that there is at least some evidence to support the view that the velocity of light is constant with respect to the source and that this would resolve the dilemma presented to physics by the Michelson-Morley experiment. As physics has not accepted this path one can logically assume that there must be overwhelming evidence to the contrary which supports the postulate that the velocity of light is always constant independent of the velocity of the source. I have looked in vain for such evidence: most books seem to manage without any, the only evidence I have found being de Sitters' observation of double stars. If the whole of modern physics is based only on that I think we should all be worried.

The standard technique seems to be to ignore Doppler and aberration, to fudge the evidence in respect of the postulate and dive straight into the mathematics of relativity.

From this appear the relativistic Doppler shift equation and aberration equation. Thus having shown that both are embraced by relativity one never has to ask the questions I have raised. Now the relativistic Doppler equation may be written.

$$\frac{f_o}{f_s} = \left(\frac{c-v}{c}\right) \left(\frac{1}{\sqrt{1-v^2/c^2}}\right)$$

The second term is time dilation, which for modest values of v is equal to unity. My question is what is the physical mechanism which produces the first term which appears to be the ratio of two velocities. If the velocity of the wave is the same to both observers there is effectively only one other possible variable and that is time (note distance can be defined as the distance travelled by a light beam in unit time) so that if the first term is not due to a difference in velocity of wave it must be due to a time difference or time dilation. Both observers observe the same wave. They both observe that it is travelling at the same velocity yet they disagree as to its frequency because their clocks are ticking at a different rate. But whose clock is ticking faster. It depends on which observer is sourcing the beam of light. If both send a beam to the other simultaneously then we get the mathematical absurdity.

$T_A > T_B$  and  $T_A < T_B$  - both true.

This type of "paradox" has been mentioned in *WW* before, but surely either the result must be rejected because it doesn't conform to the laws of mathematics, or the laws of mathematics are wrong, in which case the derivation of the result must be rejected as being based on faulty mathematical laws.

I would welcome any suggestions as to where I am going wrong.

## Appendix Double Stars

For those unfamiliar with this piece of evidence the idea is that if the velocity of light was constant with respect to the source then the light from a star in a binary system which is travelling towards us would tend to overtake that from the

star going away from us with the result that their observed orbits would seem irregular. De Sitter observed double stars and no orbital irregularity. I have yet to find out when or where these observations took place, the magnitude of the expected irregularity, de Sitter's measurement accuracy, and why he didn't get a Nobel prize for this obviously vital work.

J. Kennaugh  
Cornwall

## DIMENSIONS

The arguments which appear in the letters to *Wireless World* month by month on the validity and meaning (if any), of D and B, E and H, the products of  $\mu$  and  $\epsilon$  and the ratio of  $\mu$  and  $\epsilon$ , seem never ending. As a student in the late 1940s I was obliged to learn such formulae and their "dimensions" in e.m. units, e.s. units and Gaussian units from the famous text books of S. G. Starling. The apparent duality of e.m.u. and e.s.u. systems and their quaint skew symmetry appealed to the mystics who mused on the inner meaning of the symmetries. At that time the main practical use to me was as a means of checking half-remembered formulae in examinations!

With the introduction of S.I. units, the theory of dimensions seems to have fallen into disuse or was considered 'not quite decent', except in the pages of *Wireless World*.

In the early 1950s, while designing and testing waveguide components, I was very impressed with the frequency with which the expression  $(\sqrt{\mu\epsilon}) = Z_0$  appeared in texts dealing with waveguides and aerials and the concept that  $Z_0$  was the characteristic impedance of free space for plane e.m. waves appealed to me. I remember noticing that if one listed such properties as charge, "magnetic pole", electric field, B and D, E and H and so on, with their e.m.u. and e.s.u. dimensions in separate columns, most of the e.m.u. dimensions occurred in powers of  $\epsilon^{1/2}$  or  $\epsilon^{-1/2}$  while the e.s.u. dimensions of that property was usually expressed in corresponding powers of  $\mu^{-1/2}$  or  $\mu^{1/2}$ .

I then made up a third column in which the dimensions were the geometric means of the dimensions in the e.m.u. and e.s.u. columns, expecting to find an inconsistency, but to my surprise I found this was also a self-consistent system of dimensions in which the "4th dimension" was  $(\sqrt{\mu\epsilon})$ , which I have denoted by Z in Table 1. Symmetry was greatly improved. The skew symmetry between e.m.u. and e.s.u. di-

mensions of analogous magnetic and electric properties had now vanished, so far as ML and T were concerned, and only appeared as opposite sign in the index of Z. I therefore added a 4th column in M,L,T and Y, where  $Y=Z^{-1}$ . The skew symmetry now reappears, but with no mystery, as *WW* readers have been considering the duality of networks expressed in terms of impedance and admittance for a very long time!

It would now seem that the duality of magnetic phenomena and electric phenomena has a very close affinity to that duality used in networks expressed in Z and Y. At this stage, I discovered that Fitzgerald had known about the M,L,T,Z system of dimensions in the late 19th Century but was unable to identify Z which he regarded as a "slowness" or "retardation" of some kind. So Fitzgerald abandoned the concept. The Z system of dimensions does not derive logically from inverse square laws of forces between magnetic poles and electric charges which many people regard as impossible experiments, anyway.

So far, I have never found any inconsistencies in the Z system outlined here and would be obliged to readers who can point any out to me. I have unfortunately now lost the reference to Fitzgerald's paper which may have appeared in an early series of *Proc. Roy. Soc. or Phil. Mag.* in the 1890s. Can anyone help?

It is well-known that despite similarity in the mathematical methods from which they are derived, resistance and reluctance are not analogous electric and magnetic phenomena. This is demonstrated in Table 1 in e.m.u., e.s.u. and also in Z systems of dimensions. I am inclined to believe that more attention should be paid to the nature of Z and the dynamic properties of e.m. radiation, following Maxwell, rather than tackling static properties like  $\mu + \epsilon$ , derived from impractical hypothetical experiments. A change from mass to 'spin' or 'action' is also interesting for simplifying charge and 'magnetic pole', B + D and flux.

Whether the Z system will throw any light on the problems of your correspondents is incalculable; all I can hope is that by throwing yet another pebble into the pond perhaps some other obscuring ripple may be temporarily cancelled out, allowing a momentary glimpse of the underlying physics before too much mud is stirred up!

E. F. Dawson  
Melton Mowbray  
Leicestershire

TABLE 1

Property	Dimensions in ESU	Dimensions in EMU	Geometric mean of ESU & EMU $Z = \sqrt{\mu\epsilon}$	$Y = Z^{-1}$
charge	$M^{1/2}L^{3/2}T^{-1}\epsilon^{-1/2}$	$M^{1/2}L^{1/2}T^{-1}\mu^{-1/2}$	$M^{1/2}L^{1/2}T^{-1/2}\epsilon^{-1/4}\mu^{-1/4}$	$M^{1/2}L^{1/2}T^{1/2}\epsilon^{1/4}\mu^{1/4}$
magnetic pole	$M^{1/2}L^{1/2}T^{-1}\epsilon^{-1/2}$	$M^{1/2}L^{3/2}T^{-1}\mu^{-1/2}$	$M^{1/2}L^{1/2}T^{-1/2}\epsilon^{-1/4}\mu^{1/4}$	$M^{1/2}L^{3/2}T^{1/2}\epsilon^{1/4}\mu^{-1/4}$
electric field E	$M^{1/2}L^{-1/2}T^{-2}\epsilon^{-1/2}$	$M^{1/2}L^{-1/2}T^{-2}\mu^{-1/2}$	$M^{1/2}L^{-1/2}T^{-2}\epsilon^{-1/4}\mu^{-1/4}$	$M^{1/2}L^{-1/2}T^{2/2}\epsilon^{1/4}\mu^{1/4}$
magnetic field H	$M^{1/2}L^{-3/2}T^{-1}\epsilon^{-1/2}$	$M^{1/2}L^{-1/2}T^{-1}\mu^{1/2}$	$M^{1/2}L^{-1/2}T^{-1/2}\epsilon^{-1/4}\mu^{1/4}$	$M^{1/2}L^{-3/2}T^{1/2}\epsilon^{1/4}\mu^{-1/4}$
B	$M^{1/2}L^{-1/2}T^{-1}\epsilon^{-1/2}$	$M^{1/2}L^{-1/2}T^{-1}\mu^{-1/2}$	$M^{1/2}L^{-1/2}T^{-1/2}\epsilon^{-1/4}\mu^{-1/4}$	$M^{1/2}L^{-1/2}T^{1/2}\epsilon^{1/4}\mu^{1/4}$
D	$M^{1/2}L^{-1/2}T^{-1}\epsilon^{-1/2}$	$M^{1/2}L^{-1/2}T^{-1}\mu^{-1/2}$	$M^{1/2}L^{-1/2}T^{-1/2}\epsilon^{-1/4}\mu^{-1/4}$	$M^{1/2}L^{-1/2}T^{1/2}\epsilon^{1/4}\mu^{1/4}$
$\mu$	$M^0L^{-2}T^2\epsilon^{-1}$	$M^0L^0T^0\mu^1$	$M^0L^{-1}T^1\epsilon^{-1/2}\mu^{1/2}$	$M^0L^1T^{-1}\epsilon^{1/2}\mu^{-1/2}$
$\epsilon$	$M^0L^0T^0\epsilon^1$	$M^0L^{-2}T^2\mu^{-1}$	$M^0L^{-1}T^1\epsilon^{1/2}\mu^{-1/2}$	$M^0L^1T^{-1}\epsilon^{-1/2}\mu^{1/2}$
electric resistance R	$M^0L^{-1}T^1\epsilon^{-1}$	$M^0L^1T^{-1}\mu^1$	$M^0L^0T^0\epsilon^{-1/2}\mu^{1/2}$	$M^0L^0T^0\epsilon^{1/2}\mu^{-1/2}$
capacitance	$M^0L^1T^0\epsilon^1$	$M^0L^{-1}T^0\mu^{-1}$	$M^0L^0T^0\epsilon^{1/2}\mu^{-1/2}$	$M^0L^0T^0\epsilon^{-1/2}\mu^{1/2}$
inductance	$M^0L^1T^0\epsilon^{-1}$	$M^0L^{-1}T^0\mu^1$	$M^0L^0T^0\epsilon^{-1/2}\mu^{1/2}$	$M^0L^0T^0\epsilon^{1/2}\mu^{-1/2}$
magnetic reluctance	$M^0L^{-1}T^2\epsilon^1$	$M^0L^{-1}T^0\mu^{-1}$	$M^0L^{-1}T^1\epsilon^{1/2}\mu^{-1/2}$	$M^0L^1T^{-1}\epsilon^{-1/2}\mu^{1/2}$

## AERIALS AT SEA

Regarding Wiseman's articles on marine radio, it is unfair to compare Soviet merchant practice with the West's since all Soviet ships are quasi-military and under strict government control, hence "proper" aerials.

I agree that some of the installations are quite appallingly bad and have been neglected, but the root cause is the short aerial, and lack of radiation resistance. Since we cannot emulate the BBC's "big T" at Droitwich within the confines of a ship another solution must be found, and I suggest that the helically loaded glass-fibre whip is the answer. Glass-fibre poles are freely available (pole vaulters use them). Such poles are about twenty feet long and would accommodate around one hundred metres of 16 s.w.g. copper wire. Since these aerials could be manufactured to have a driving-point impedance equal to that of the feeder, insulation losses would be minimal.

Regarding the durability of glass-reinforced plastics, cheap g.r.p. is based on polyester resin, which is hygroscopic and does deteriorate in the space of a few years. G.r.p. reinforced with epoxy resin does not appear to suffer in this way although it is more costly.

Finally if anyone is enterprising enough to make such an aerial, he must be sure to avoid a carbon fibre reinforced pole.

D. Benyon  
Bude  
Cornwall

## HERETICS GUIDE TO MODERN PHYSICS

I would have thought that authors prepared to advertise their Ph.D., B.Sc., and so on would show a more up-to-date knowledge and greater scientific integrity than that displayed in October 1982 *WW* by Dr Scott Murray.

The 'Photon' article revolves round and leads to a conclusion that a special test experiment on counting single photons should be done, and the author confidently predicts the result that individual photons passing through an apparatus would not show interference. I'm afraid that Scott Murray is out of date by 50 years or more; the experiment has been done many times, since photon counters (able to detect single photons) have been available for a long time. And the result - individual photons produce interference fringes just as more intense light does.

I cannot offer an explanation, since apart from using quantum mechanics (which is a mathematical description) there is no explanation in mechanistic terms of what happens. The problem strains our imagination to its limits, but explanation or not, it is a hard experimental fact. I do not think that this can be passed off as a subjective assessment as implied by John W. T. Smith, September, 1982 *WW* letters), since the photomultiplier either does, or does not register photons at certain position along the interference fringe pattern. This experiment has been repeated by many workers, since the topic is of great significance, yet always the same result.

I think therefore Scott Murray should review the contents of any subsequent articles on this theme if they rely on his incorrect anticipation of the photon experiment. A good description of this experiment occurs in Richard Feynman's Book - *The Character of Physical Law* (BBC Publications 1966).

To further confound Scott Murray, electrons also show wave/particle duality and give interference fringes too; this is also described in Feynman's book.

One further point, articles of a scientific nature, whether 'heretical' or not, are improved by less use of emotive terms like 'dogma', 'mysticism' 'doctrine'. It would seem that the only person with a dogmatic view is Scott Murray himself who has decided to shun the facts and invent his own 'nature'.

B. J. C. Burrows  
Benson  
Oxford

In the article from the series by Dr Murray which appeared in the December issue he refers to Compton's calculation of the way in which the energy of a gamma ray scattered by a free electron varies with the angle of scattering, though for some reason he describes the scattered gamma ray as a second gamma radiated from the point of impact. He claims correctly that Compton's calculation was based on the model of a billiard ball collision between the gamma ray photon and the electron, but neglects to mention that this model is quite unable to account for the experimental observations of the angular distribution of the scattered photons about the direction of the incident photons. Eventually Klein and Nishina succeeded in deriving an expression for this distribution which is accurate up to and beyond energies of 10 MeV, but they made use of wave mechanics. So much for his assertion that there is 'no indication of wavelike properties of either electrons or photons'.

He goes on to discuss the photo-electric effect. This effect, in which an incoming gamma ray is completely absorbed by a single atom, which then emits a single electron carrying the excess energy, has been studied for many years. Characteristically the electron has a distribution about the direction of the gamma ray which extends over a wide range of angles, and an energy which falls short of that of the gamma ray by an amount which has a series of discrete values determined by the atom from which it is ejected'. Thus the process observed experimentally bears little resemblance to the results of Dr Murray's calculation, since according to him 'the direction of the electron's motion must be at right angles to the incident photon's path to within a few hundredths of an angular degree'. Even if one were to take Dr Murray's calculations at their face value, and to accept that they would apply to the photons associated with electromagnetic waves, a 'Murray photon' hitting a vertical dipole aerial would be equally likely to eject an electron from its parent atom so that it moved towards the top, bottom, or sides of the aerial rod, giving zero net induced current!

In general a photon will interact collectively with electrons in an area of the wave front with linear dimensions of at least one wavelength. For the optical photo-effect, in which a photon of visible light ejects a single electron from a suitably prepared surface, the wavelength is some tens of interatomic spacings, so that despite the end result the effect cannot be explained in terms of the interaction of the photon with an isolated electron or atom. A 300 MHz photon, whose energy is some  $10^{-9}$  eV only, would interact collectively with electrons over the whole length of a dipole aerial tuned to that frequency, though I doubt whether individual quantum phenomena as such have been ob-

served at frequencies below 300 GHz. This is hardly the behaviour of a classical particle, and it is not surprising that Dr Murray turned his discussion rather quickly from photons and electromagnetic waves to the consideration of much higher energy photons.

The articles in the series so far have either been written tongue in cheek, or betray a failure to grasp the basic ideas of quantum mechanics and a very limited knowledge of the experimental results which confirm some of its most radical predictions. It is rather unfortunate that *Wireless World* should be propagating this 'disinformation' at the very time when experiments are coming down solidly in favour of one of the most mind-blowing of these predictions, one which is at variance even with the simpler versions of Special Relativity<sup>2</sup>.

C. F. Coleman  
Grove  
Nr. Wantage  
Oxfordshire

## References

1. C. M. Davison, 'Interaction of  $\gamma$ -Radiation with Matter', from 'Alpha-, Beta-, and Gamma-Ray Spectroscopy', Ed K. Siegbahn, North Holland, Amsterdam 1965.
2. A. Aspect, P. Grangier and C. Roger, *Phys. Rev. Letters* 47 (1981) 460. R. D. Mattuck, *Eur. J. Phys.* 3 (1982) 107.

Dr Scott Murray (Quantization and quantization, Jan. 83) regards the idea that light seems to consist sometimes of waves and sometimes of particles to be mysticism of the most blatant kind. Indeed it would be if one believes that light 'consists' of waves and particles, since these two entities have mutually exclusive properties.

The idea that any physical phenomenon 'is' or 'consists' of either waves or particles is surely the root of the problem. The concept of wave and of particle are pure abstractions. They summon up in each case a set of mathematical relationships which define what we mean by these abstractions. A bullet or a billiard ball do not 'consist' of particles, nor do ripples on a pond or vibrations in a plank of wood 'consist' of waves. That the abstract set of ideas associated with waves is useful in describing and predicting certain physical events, like the movement of a violin string is true. Similarly, the set of ideas associated with particles is clearly of value in other areas. That light has some properties for which the wave concept is more useful, and other properties for which the particle concept is of greater value presents no contradiction. It simply demonstrates that we have yet to devise a unified, internally consistent set of ideas which are paralleled in the physical world by all of light's manifestations.

M. M. Gleave  
Whitstable  
Kent

I have an increasing sense of bewilderment on reading Dr W. A. Scott Murray's series of articles so far.

I may be simple-minded, but I am unable to see that certain of Dr Murray's remarks have the remotest connexion with any physical phenomena ("... prediction is foreign to Nature..."), "... living matter... does this (build enzymes etc. for its own convenience) by decreasing entropy locally...").

Now Dr Murray unveils what seems to be his fundamental physical paradigm, of "discrete

physical entities having real, free-standing existence independently of each other and of any observer, human or deputy." Such a paradigm fails to provide any account even of the simplest interactions between such "entities", and I am afraid it suffers the same fate as all other attempts to explain the obscure in terms of the more obscure.

Indeed, this must be the fate of all attempted explanations which may be produced in accordance with Dr Murray's own criterion of demarcation between physics and mysticism (physical phenomena to be physically explained). Thus, any such attempted physical explanation will involve physical phenomena; but the criterion demands that these be explained physically, and so we either end up with an infinite regress (or a circularity) of physical explanations, or finish after all with something that is not explained at all, or at least not physically! I think we need a better criterion than what Dr Murray has proposed!

In summary, I am afraid that Dr Murray seems to show basic confusion about what is and is not capable of being meant and explained by a physical theory. I am unable to say what is the essence of a better approach to making, using and understanding theories, but anybody who would like to arrive at such an approach could do very well, I believe, to consider the views of Sir Isaac Newton. I quote his refusal to speculate on the nature and origin of the interactions involved in the phenomena of universal gravitation, for which he had provided his celebrated mathematical account: (Concerning such matters) "I frame no hypotheses; for whatever is not implied by the phenomena is to be called an hypothesis; and hypotheses, whether physical or metaphysical, whether of occult things or mechanical, have no place in experimental philosophy."

Newton's 'experimental philosophy' is none other than what we now call science. I suggest that 'hypotheses, whether physical or metaphysical...' also have no place in a scientific journal such as *Wireless World*.  
Terry Stancliffe  
Wimbledon  
London SW19

**The author replies:**

Readers' letters in response to the "Heretic's Guide" series so far have fallen into two categories: the interested and constructive ones have mostly been addressed to me privately and some of them have initiated encouraging correspondence, while the critical and sometimes personally-abusive ones have tended to be addressed to the Editor of *Wireless World* - occasionally even taking him to task too for allowing such nonsense to be published in his magazine! That pattern was predictable and I have no fault to find with it.

One of the recurring topics is the suggestion that the interference of light might disappear at a sufficiently low light level or photon density. What is a "low" photon density? How long is a photon? (A. H. Winterfield, Letters, January). I know of several standard "experimental" answers to that second question, all of them wrong in that they are in conflict with other experimental results. Mr B. J. C. Burrows' letter may be quoted as representing the majority view on this issue. He says that "Scott Murray is out of date by 50 years or more... individual photons produce interference fringes just as more in-

tense light does... This experiment has been repeated by many workers, always with the same result."

Now the interesting point about this quote is that what Mr Burrows says, although straight down the centre of the established duality doctrine, is not in fact true. Two Russian experimenters, Dontsov and Baz' (Soviet Physics JETP, translated, 25, pp. 1-5, 1967) reported that "photons in light beams are correlated to a considerable degree and cannot be considered statistically independent as a rule... the impinging beams contained 'bunches' of photons"; and after they had dealt with this bunching (their choice of word, independently of mine), "the beam of statistically independent photons passed through the interferometer without producing an interference pattern."

One part of this experiment was quickly repeated by G. T. Reynolds of Princeton and reported at a symposium at Imperial College in 1969. Reynolds did not observe any deterioration of his interference fringes, but although he had attempted to reproduce the Russians' apparatus exactly he used a different kind of light source and his experiment was not performed in quite the same way. The most important difference was that Dontsov and Baz' had taken particular care to quantify photon bunching and to minimize its incidence, but Reynolds and his colleagues simply assumed that their photons were statistically independent at the light levels they used.

Therefore, despite Mr Burrows' disagreement, in view of this conflict of experimental findings I still feel that it would be worthwhile to perform at least one more experiment of this general type, taking special anti-bunching precautions and using photon-detection techniques effectively 100 times more sensitive than those of Dontsov and Baz', and Reynolds.

To reply fully to Mr C. F. Coleman would require a letter of at least article length, so instead let me pick out one representative passage for comment. In his third paragraph he says, "In general a photon will interact collectively with electrons in an area of wave front with linear dimensions of at least one wavelength. For the optical photo-effect, in which a photon of visible light ejects a single electron from a suitably prepared surface, the wavelength is some tens of interatomic spacings, so that despite the end result the effect cannot be explained in terms of the interaction of the photon with an isolated electron or atom."

Once more this is *ex cathedra* doctrine, faithfully reproduced.

**Comment one.** The terms photon, wave-front and wavelength appear without differentiation in that single first sentence. Here we have Duality supreme: none of the "sometimes behaves like particles" and "sometimes behaves like a wave system" of the doctrine's more cautious apologists. Here light is both at the same time. Even among Copenhagen's adherents, not every one will support this extremist line in public.

**Comment two.** The photon is said to interact collectively with electrons over a linear dimension of at least 10 inter-atomic spacings; given one free electron per lattice atom there will be 100 of them per square wavelength, or up to 1000 of them would be involved if the photon were to penetrate into the material to a depth of just one wavelength. Now, if some 100 to 1000 electrons are interacting with one incoming photon, why is it that only one of these electrons is ejected by the photon's impact - and what

physical mechanism determines which of the electrons is to be ejected? (Please don't tell me that it is ejected from the material by a "probability"! This was the very argument that in Einstein's hands in 1905 denied the possibility of a statistical mechanism for the photoelectric effect and led directly to the photon hypothesis. Are we to go back on that hypothesis now? (I don't say we shouldn't - I just ask the question).

**Comment three.** The first sentence in the quotation makes a flat statement of what happens in a photon/photocell interaction, all cut and dried as if it were factually true. How wide is a photon, please? If we knew the answer to that we might be able to "explain the effect" in line with "the end result". Many answers have been proposed to that question, all different and mutually conflicting: it is conventional nowadays to regard the question as "improper" and refuse to recognise it. But in that case perhaps I may reasonably ask instead for a reference to the report of the experiment which measured the diameter of a photon and supports the statement that it is "at least one wavelength" across? I believe there is no such reference; that is one of the fundamental experiments that I have suggested ought now to be done.

Other comments could be made, but perhaps I have said enough. There are many things in the arena of modern physics that none of us understand, and it doesn't help progress for people to insist that we know it all when in fact we don't. It is more seemly to be humble when discussing such difficult problems. Several correspondents such as N. M. Gleave, John W. T. Smith and Professor D. A. Bell have written in a very civilized way on the theme that "... we have yet to devise a unified, internally consistent set of ideas which are paralleled in the physical world..." (with which I wholeheartedly agree), and that it may never prove possible to devise one because the scope of human thought-processes may be too limiting. There is as yet no evidence of this either way, but it suits my temperament to be optimistic. What I don't go along with is the idea that one should give up trying to understand such things simply because the Copenhagen School, having themselves failed to reach understanding of them, arrogantly pronounced them to be non-questions, unsuitable for the attention of physicists. It is just possible that the Copenhagen School and their followers may have been wrong on that point, as they have been on quite a few others.

I move that we should re-examine our current physical concepts carefully and conscientiously in the light of a few realistic principles ("acceptable paradigms", if you will, *pace* Mr Terry Stancliffe!), and go on trying.

## SATELLITE TV SYSTEM

Dr Tomlinson, no doubt, will correct me if I am wrong but his "original method" of digital/analog modulation (*WW* January 83, pp28,29) seems to me to be a development of the ADAM modem which Freddie Court of SRDE devised, in 1971/72, during his work on SKYNET.

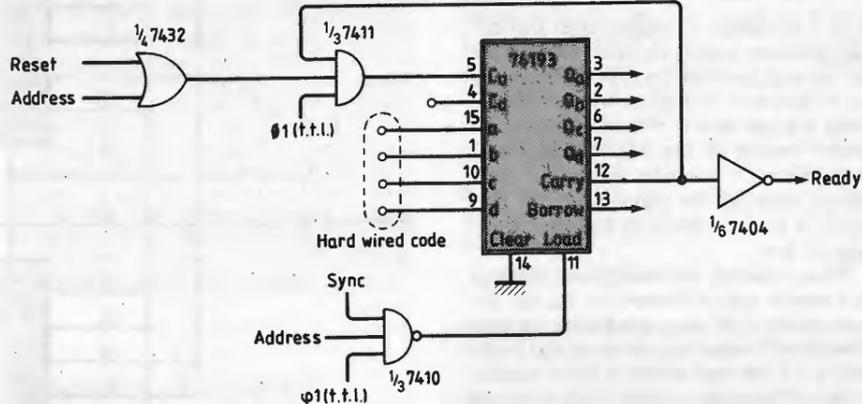
Working from memory, I believe ADAM stood for "Amplitude, Dipolar Angle Modulation".  
G. R. Miller  
Orpington,  
Kent.

## Using the 8080 with slow memories

Forcing the 8080A microprocessor to enter an adjustable wait state when addressing slow memory devices, this circuit compensates using a 74193 up/down counter. When the system starts up, the reset signal is forced high for a short period by the reset button. This period is long enough to allow 16 clock pulses ( $\phi 1$  t.t.l.) to be passed to the  $C_U$  input of the 74193 counter if the carry input of the counter is in the high state, i.e. the data output is not in the F (hexadecimal) state.

These clock pulses drive the counter to the F state when the carry output goes low. This sends the counter  $C_U$  input low and sets the ready signal to the 8080. Clocking the counter while resetting the system gives the same results as starting up the system with F as the counter-data output.

When the 8080A c.p.u addresses slow memory devices, the address is sent during the first state of the current machine cycle



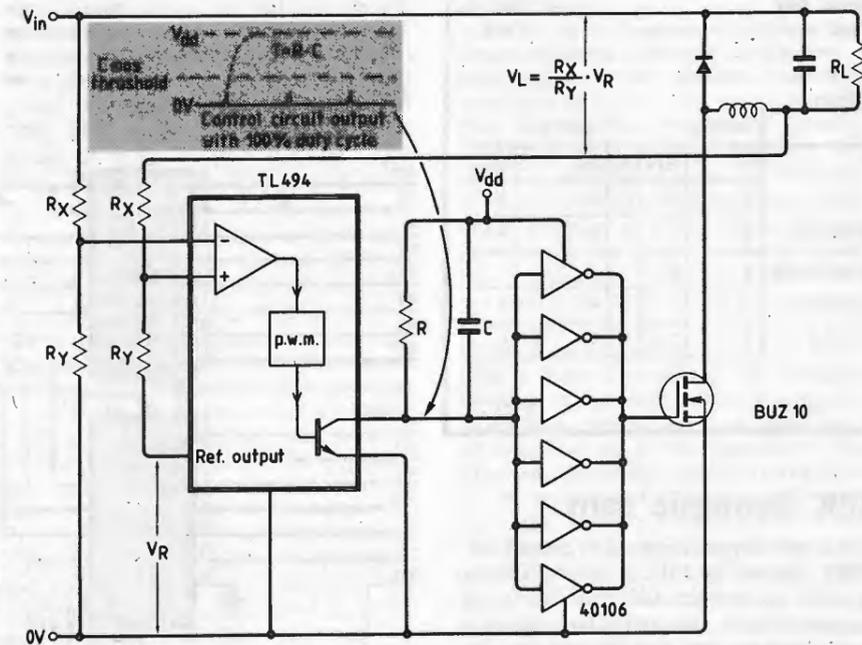
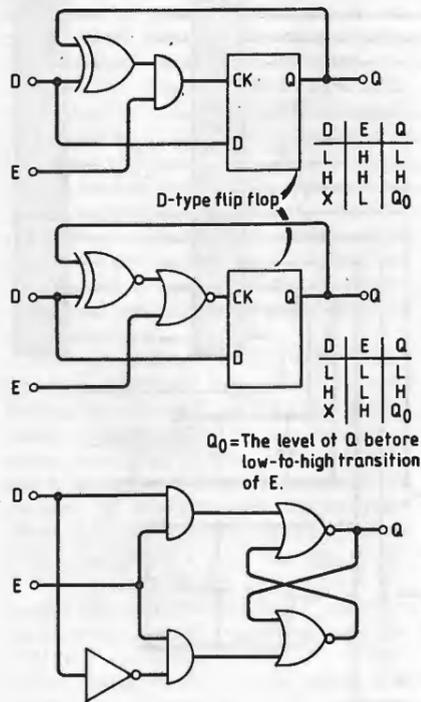
and decoded as an active-high line which drives the converter. At the start of the second machine cycle, the counter load input goes low, causing a hard-wired word at the counter data input to be loaded. Through loading of this word (which should not be F)  $C_U$  goes high, resetting the ready signal and driving the processor into a wait state. From the third machine

cycle, the counter is incremented by one until the output is F, when carry goes low and sets the ready line. Depending on the hard-wired word, the wait state can be extended between one and 15 machine cycles.  
G. A. M. Labib  
Heliopolis  
Egypt

## Alternative latches

Logic circuits often have spare gates. Where latches are required, these two circuits may help to reduce the number of i.cs in a given design. Their standard equivalent is also shown.

Y. Pang  
Worthing  
W. Sussex



## Switching regulator with 0-100% duty cycle

Designed for low-voltage battery-powered systems, this efficient switching regulator relies on a power mosfet's low drain-source resistance. Controllers available have duty cycles less than 95% so the switching element cannot fully conduct with low input voltages. This circuit uses an RC pulse

stretcher to give a 100% duty cycle. Multiple cmos gates provide sufficient power to drive an n-channel fet with low  $R_{ds(on)}$ . To include this device, the standard switch-mode circuit is inverted. Care must be taken not to exceed the common-mode range of the control-circuit op-amp.  
Bryan Inkster  
Egersund  
Norway

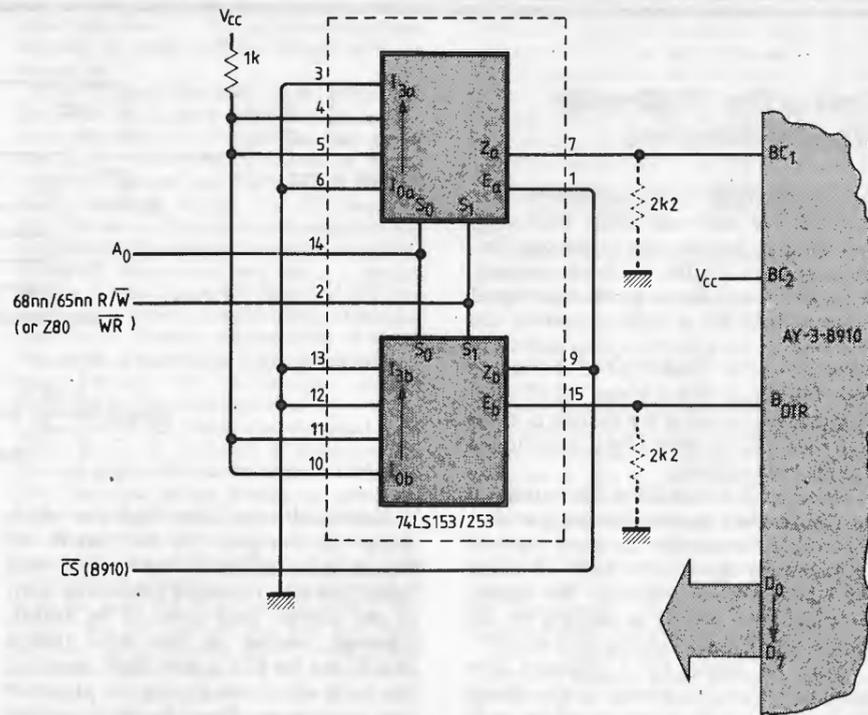
## Sound-generator interface

With a minimum of components, this circuit produces signals required to interface the General Instruments AY-3-8910 sound i.c. to standard 8bit microprocessor buses using a single m.s.i. - t.t.l. device. The output enable of the 74153 dual 4-to-1 multiplexer i.c. provides an inactive bus-control state for the sound-generator i.c., which is disabled when its bus-control inputs are low.

When selected, the multiplexer behaves as a simple rom addressed by  $A_0$  and the state of the R/W line, producing outputs determined by the logic levels on the 74153 inputs. In use, one writes the port address to an odd location and one reads or writes data from an even location.

Resistors shown are pull-downs required if a 74LS253 is used, as this is a three-state output device. A version using a 74LS253 has successfully been used on a 4MHz Z80A system where it was mapped as an i/o port, the auto-wait state feature of the Z80 i/o request ensuring that the timing of signals is longer than the minimum specified in the data sheet. Another has been built into an M6809 system.

M. James  
Herne Bay  
Kent



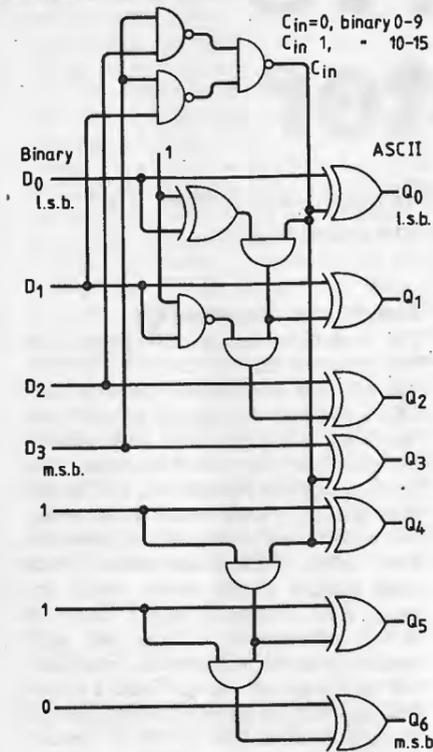
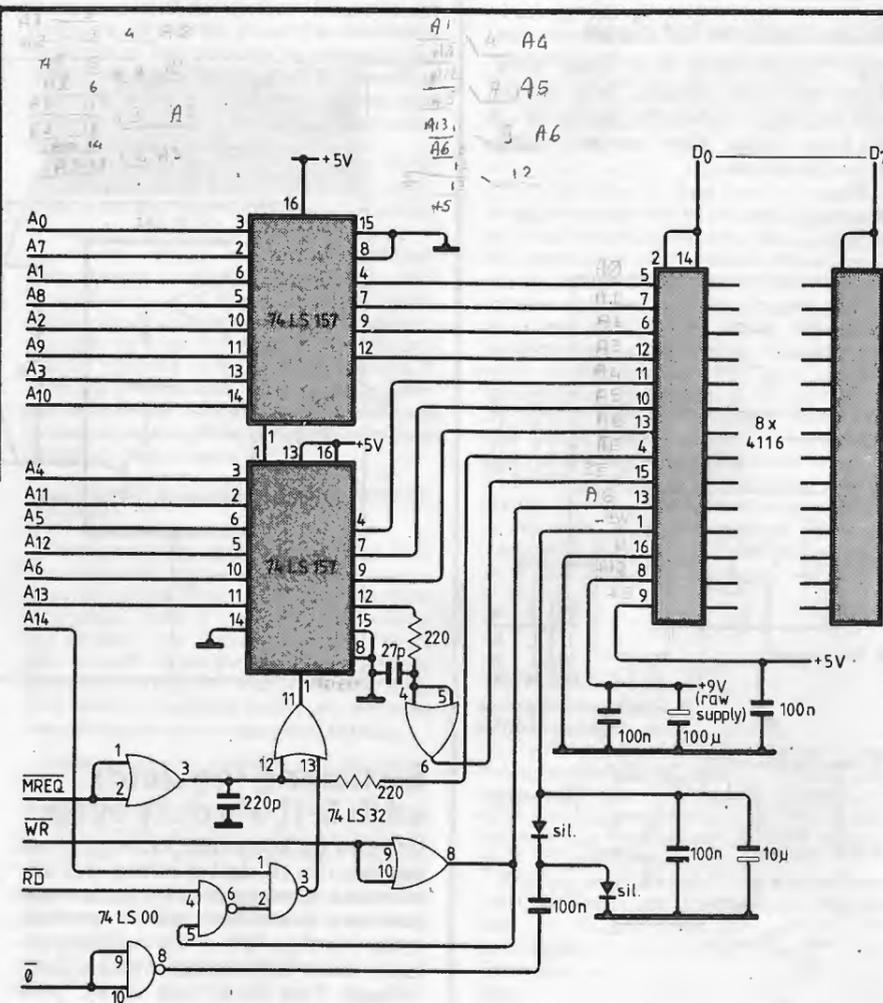
	INPUTS			OUTPUTS	
	$\overline{CS}$	R/W	$A_0$	BC <sub>1</sub>	B <sub>DIR</sub>
Write date	1	X	X	0	0
Write address	0	0	0	1	1
Read data	0	1	0	1	0
Inactive	0	1	1	0	0

## 16K dynamic ram

Cost of this circuit, designed to expand the ZX81 memory by 16K, is around £10 as opposed to between £25 and £50 for a commercial unit. Illustrating how easy it is to use dynamic ram, this memory may be used with any Z80 system with only slight modifications. I did not need a case since my computer is in a large box.

Negative bias, generated by a NAND gate, capacitor and diodes, is only around 3V but this is sufficient. Positive supply to pin 8 of the 4116 rams is taken from the raw supply, hence the 100µF smoothing capacitor.

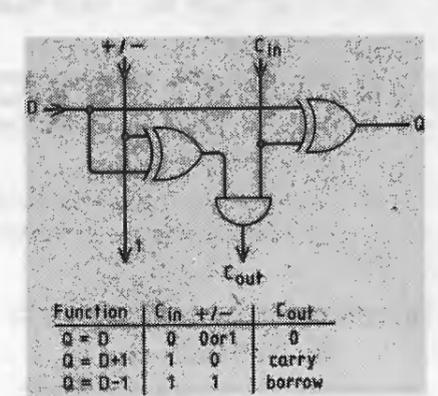
D. G. Jones  
Leamington Spa  
Warwickshire



## Cascadable one-bit arithmetic module

The module shown adds one, subtracts one or transfers the input to the output. Cascaded modules, with  $C_{out}$  connected to  $C_{in}$  of a more-significant module, operate with binary-weighted inputs giving

$$Q_0 2^0 + \dots + Q_7 2^7 = D_0 2^0 + \dots + D_7 2^7 + N$$



where N is plus one, minus one or zero. There are two control inputs,  $C_{in}$  which selects add/subtract or transfer, and  $+/-$  which selects add or subtract. When operation is limited to  $+/- = 1$ , gate<sub>1</sub> may be any inverter and when  $+/-$  is limited to zero, gate<sub>1</sub> may be omitted. The binary-to-ASCII circuit uses  $+/- = 1$  for bits zero to two and  $+/- = 0$  for bits four to six.

R. Merson  
Taunton  
Somerset

Dividing by fractions. Some readers have found the 4722 timer used in this circuit idea (Jan 1983) difficult to obtain. The 4722 may be replaced by an XR-2240 (Exar) or a µA2240 (Texas) without circuit modifications. An XR2212, XR215 or NE565 may be used in place of the p.l.l.

continued from page 35

in terms of continuity - that the potential can always be described in terms of position by means of a smooth, broadly-generalized mathematical curve. A barrier of this type must obviously be completely leak-proof, but this is not what is observed in Nature. The concept may sometimes suffice to describe the behaviour of matter in bulk, but it fails to take into account the essential granularity of matter on the microphysical scale. These barriers are composed of particles. The often-quoted tunnel effect is not to be explained as a manifestation of matter waves, mystically, but by a down-to-earth study of the physical properties of the particles involved as particles, and of the real, physical forces that act between them. The insulator is not quite impervious to current, nor the radioactive nucleus quite stable, given time. That is what the quantum hypothesis implies, and its realisation defines the coverage required of any successful quantum theory of matter.

Now the failure of the wave theory which is evidenced here is a conceptual failure, far more serious than any expositional or mathematical failure. Instead of being just wrong the theory is seen to be utterly wrong, because it is based on the concept of continuity in microphysics which although mathematically convenient is by experiment a false concept. It has failed, in fact, for the same reason that caused electromagnetic theory to fail when faced with Planck's quantization (type one) and its obverse, the photoelectric effect. Moreover there would seem to be no prospect of recovery in either case, because continuity and discontinuity are dia-

metrically opposed in logic: any true quantum theory must therefore be the antithesis of any field theory.\* But whereas electromagnetic theory often provides good and useful analogies, the wave theory of matter consistently offers bad ones. Over and over again we have been misled by it. It has proved to be a bad habit. Should we not consider giving it up?

Probably the most insidious of all Copenhagen doctrines is the doctrine of Completeness, which was concocted from the doctrine of the Observer with the aid of a liberal sprinkling of Indeterminacy. The idea was that as Nature is indeterminate and essentially statistical, and as (quoting Landé before his conversion) it is "unphysical" to dwell on situations that can never be observed, it followed that the Copenhagen quantum theory, which incorporates these restrictions, must be "complete" - the Ultimate Theory of microphysics. Einstein challenged this doctrine on general grounds on its first formulation, but the argument was side-tracked by Bohr into a discussion of the "correctness" of the wave-mechanics (which we can now see to have been an irrelevant issue), and

\*The point may be paraphrased and repeated in view of its philosophical importance. The so-called quantum theory of Copenhagen, involving as it does the concept (and mathematical equations) of waves in a continuous medium, is essentially a field theory. As such, it can by approximation describe the behaviour of matter in bulk, but it is intrinsically unable to cope with any discontinuity or "quantum" - electron or photon. This logical contradiction, both as an expression of and as the root of the duality concept of Niels Bohr, lies at the very heart of the Copenhagen aberration.

the challenge, thus evaded, was eventually allowed to drop.

Earlier in the present sequence, and from a different standpoint to Einstein, I have argued that the premise of the indeterminacy of Nature was almost certainly false and that the observability premise was never more than a doctrinaire, and arbitrary, attitude of mind. Nevertheless, on those very dubious premises the Copenhagen doctrine of completeness claimed, grandiosely, that as this particular, peculiar, probabilistic "quantum theory" cannot explain the fundamental phenomena in microphysics, no theory can. Pulling itself up by its own bootstraps, it had the gall to offer a "logical proof" of this arrogance based on its own misguided self-restriction to statistical treatments. (I am referring to an argument by J. von Neumann). The One True Faith being unable to pronounce on the structure of the electron, it would be sacrilegious for any other theory to presume to try. Such effrontery was amazing, especially when one remembers that Niels Bohr himself had been forced to admit,

"The quantum mechanics deals not with the properties of micro-objects as such but, rather, with nothing more than the relationships between the observable, large-scale phenomena".

One can only suggest, with moderate diffidence, that a theory which was not confined essentially to macroscopic, statistical relationships might be better able to handle the encounters of individual micro-objects, while a theory that took the reality of the physical world more seriously might prove more successful in describing it. This cannot be the end of the road. WW

# Low-cost servo accelerometer

A design simple enough for home construction, yet capable of an accuracy better than 0.1% of full-scale. It can also be used as a precision force balance

In recent years analogue and digital electronics have advanced very rapidly and it is now possible to perform complex manipulations of electrical signals at low cost. Unfortunately these advances in electronics have not been paralleled by similar advances in the design of the transducers required to convert other physical quantities into electrical signals. It is particularly frustrating for an amateur to have a project which he can easily handle electronically but which is stopped by the high cost of suitable transducers.

The acceleration transducer described here was developed as part of an automotive acceleration and braking performance measuring instrument. Other potential uses include an angle-of-heel indicator for a yacht, a precision level, an earthquake detector, a vibration-type car theft alarm and a home intruder-alarm based on measuring the deflections and accelerations of the floor structure. The transducer can also be used to measure forces up to 0.1 newton (0.02lb) directly, or higher values if a suitable lever system is added. In addition to the obvious application to weighing machines the force measurement capability could also be useful for the measurement of low velocity air flows, where the drag of a small vane could be sensed, and for pressure measurements, where a flexible diaphragm could be used to convert the pressure to a force.

## Operating principle

The accelerometer described is based on the servo-balance or force-balance principle. A mass is suspended by a system of flexures which constrain it to move relative to the transducer body only in the direction of the acceleration to be measured (Fig. 1). When the transducer body is accelerated along the sensitive direction the mass will obey Newton's first law of motion and remain at rest. This will produce a relative movement between the mass and the body which is sensed by the displacement detector. The detector output is amplified and applied to an electromagnetic force generator which returns the relative movement between mass and body to zero. The net effect of this feedback loop is that the force generator always applies the appropriate force to the mass to produce an acceleration which is identical to that of the transducer body. Since, according to Newton's second law of motion, the acceleration is directly proportional to the force producing it, the force output of the

by Neil Pollock

electromagnetic generator will be an accurate measure of the acceleration. Further, since for small displacements a moving coil force generator exhibits a highly linear relationship between current and force, the current flowing in the coil will be an accurate measure of the acceleration. This current is conveniently measured by sensing the voltage drop across a resistor in series with the coil. It can be seen that an external force applied directly to the moving mass will be measured in exactly the same way as an applied acceleration.

This simple system would tend to oscillate at a frequency determined by the size of the mass and the effective stiffness of the feedback system. To ensure stability it is necessary to include some mechanical or electrical damping. It is common practice to produce at least some of the damping electrically by incorporating a phase-lead network in the servo amplifier. The servo loop should have the highest possible gain to produce the greatest effective stiffness and therefore the highest frequency response and smallest movement of the suspended mass. Minimum movement of the mass is important because the linearity of all practical force generators deteriorates with displacement. The highest gain that can be used is usually limited by stability considerations.

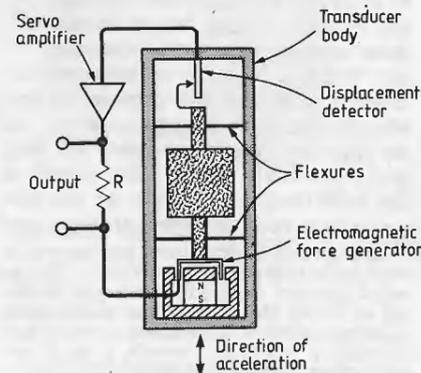


Fig. 1. Outline of the force-balance accelerometer. The e.m.f. generator acts to cancel movement of the mass resulting from acceleration of the transducer body.

## Transducer construction

The transducer design was prompted by the realisation that the magnet and voice-coil out of a loudspeaker make an ideal force generator. An optical isolator/interrupter of the type used for limit switches and end-of-tape indicators was selected for the displacement detector and the flexures were fabricated from a steel guitar string. The remainder of the transducer was made from scraps of aluminium sheet, double sided printed circuit board, solder and epoxy glue. Figures 2 and 3 show the overall arrangement. Since the loudspeakers available to potential constructors will vary in size and design detail, a general description of the construction process will be given rather than a set of detailed drawings.

The most suitable type of loudspeaker is the sort used in pocket transistor radios. The one chosen for the various prototypes had a cone diameter of about 56mm (2.25 inch), a voice coil diameter of 13mm (0.5 inch) and a resistance of 8Ω. In preparing it for use, the first step is to dismember the speaker to obtain an undamaged voice coil and magnet (Fig. 4). To do this, the braided connecting leads should be unsoldered from the voice coil where they join the cone. Then the majority of the cone can be cut away using a razor blade and small nail scissors. The corrugated diaphragm normally hidden by the cone can then be cut with a sharp razor blade. The voice-coil can then be lifted clear of the magnet and the remains of the cone and diaphragm cut away. If drilling or cutting is necessary to separate the magnet from the speaker frame, it is a good idea to stick adhesive tape over the magnet gap to prevent the ingress of metal chips. When the magnet is removed all the metal chips, filings and whiskers which will inevitably find their way into the gap must be carefully cleaned out using a needle and a compressed air hose. If everything has been done correctly the voice-coil should drop cleanly into and out of the magnet without sticking.

The next step is to construct the flexure assembly (Fig. 2 and Fig. 5). The moving mass consists of two squares of double-sided printed circuit board slightly larger than the voice-coil diameter, joined together with a countersunk brass screw. For the flexure mounting, two rectangular pieces of the same board are joined with two screws. A clearance hole for fixing is drilled in the centre of the lower piece of

board. On the upper surface of both boards of the moving mass and mounting assembly, the copper coating should be cut back from the screw holes and insulating washers used under the nuts so that the two surfaces are isolated from each other. Next, the moving mass and mounting assemblies should be placed face down on a flat surface so that the flexures, which are cut from a 0.2mm (0.008 inch) steel guitar string, can be soldered in place. The voice-coil can then be glued to the bottom of the moving mass and its two leads connected to the same surfaces as the flexures.

The base board is cut from double sided printed circuit board. This board requires a clearance hole for the voice-coil, a hole for the flexure assembly attaching screw and holes for the mounting screws and lead wires of the two opto-interrupters (Fig. 2 and Fig. 3). The magnet can then be glued to the base board with the magnet gap concentric with the voice-coil clearance hole. The flexure assembly can now be mounted with a spacer of appropriate thickness between it and the base board so that the voice coil is axially centred in the

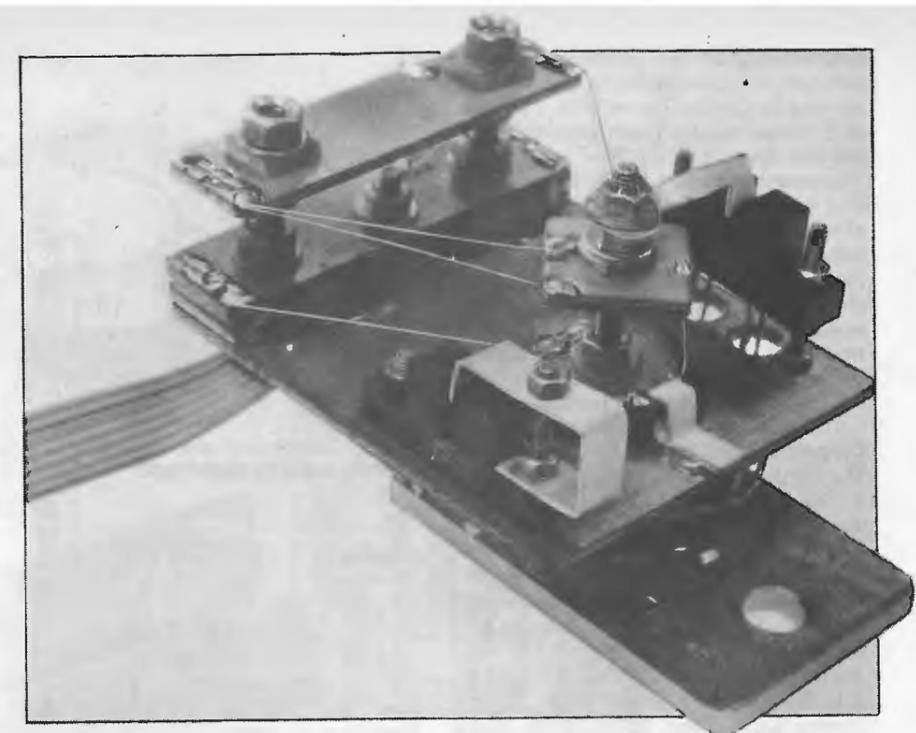
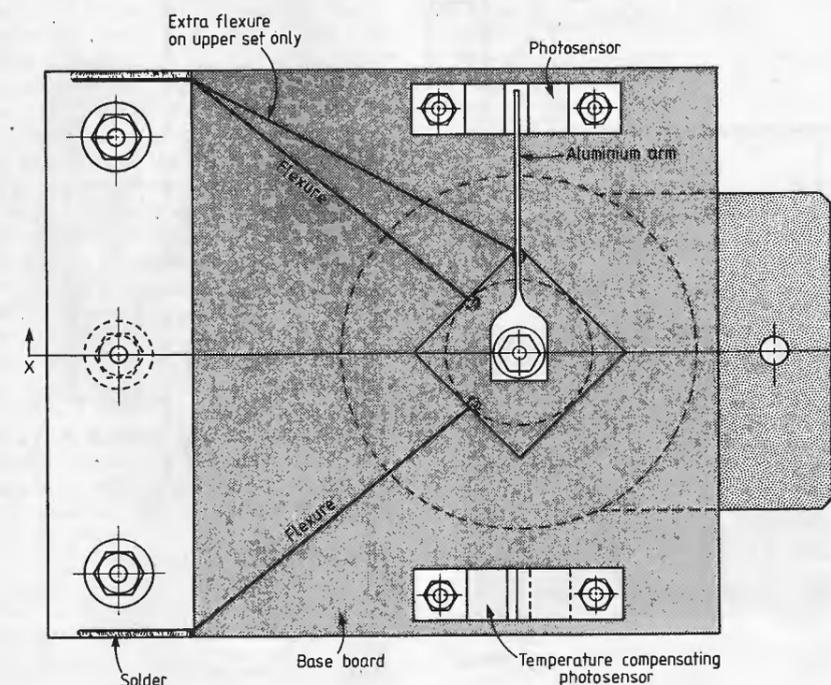
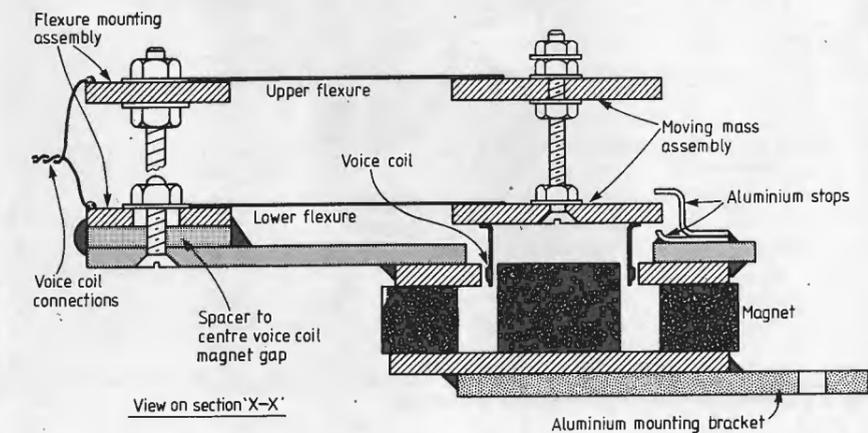


Fig. 3. Completed servo accelerometer. Potential uses include precision levels, earthquake detectors, car theft alarms and home intruder alarms. Opto-interrupter on right acts as a displacement detector; the other is for temperature compensation.



magnet gap with the flexures undeflected. The spacer thickness may be determined by measuring the various pieces prior to assembly.

Mating the flexure assembly to the base is the most critical operation in the transducer construction and the following instructions should be followed closely. Glue the spacer to the base board, then carefully lower the coil into the magnet gap. Insert the screw which secures the flexure assembly to the base and tighten it just enough to prevent the two parts sliding with respect to one another. Make small movements of the flexure mounting until the coil moves freely in the magnet without scraping. When the correct setting is achieved the moving mass will vibrate freely when the base board is stood vertically and gently shaken. At this stage the flexure mounting and base are permanently fixed together by applying a non-shrinking glue around the edges, not by tightening the screw because this will inevitably spoil the alignment and probably damage the coil.

At this stage the hardest part is over and final assembly can proceed. Two stops bent from thin aluminium sheet should be glued in place to limit the movement of the mass to about  $\pm 0.5\text{mm}$  ( $\pm 0.02$  inch) from the flexure-undeflected position. A suitable mounting bracket can be glued to the bottom of the magnet and then the two

Fig. 2. Mechanical arrangement of transducer. The e.m.f. generator is adapted from a cheap loudspeaker unit of the type used in pocket radio sets.

opto-interrupters can be fitted. The temperature compensation opto-interrupter is screwed to the base board with a pre-settable cut-off shutter made from thin aluminium sheet (Fig. 3). The active opto-interrupter is mounted on long screws so that its height above the base board can be altered easily. A thin aluminium flag attached to the centre screw of the moving mass (by tightening the nut gently and then glueing it) extends to the gap in the active sensor. When in use the transducer should be enclosed in a box, both to exclude ambient light and to prevent metal particles finding their way into the magnet gap.

### Circuit description

The circuit diagram for the servo-amplifier is shown in Fig. 6. The two opto-interrupter outputs are applied to unity gain buffers which drive a unity-gain differential amplifier. This amplifier feeds a passive lead-lag compensation network formed by  $C_1$ ,  $R_8$ ,  $C_2$  and  $R_9$  which in turn feeds a variable gain (0 to 30) amplifier. The output from this amplifier passes via Link 1 to a bridge-connected power stage. By removing Link 1 and adding Link 2, an additional amplifier can be brought into the circuit: the function of this amplifier is described below in the section on compensation. A circuit board pattern and component layout are presented in Fig. 7 and Fig. 8. It is possible to mount the circuit board either adjacent to or remote from the transducer, according to the requirements of the application. The system output, which is the voltage drop across  $R_{22}$ , is

Fig. 6. Circuit diagram of the servo-amplifier.  $IC_1$  and  $IC_2$  are quad op-amps, type LM324 or equivalent. Suitable alternatives for opto-interrupter include TIL143, TIL144 and MCT8.  $C_2$ - $C_5$  are tantalum types.

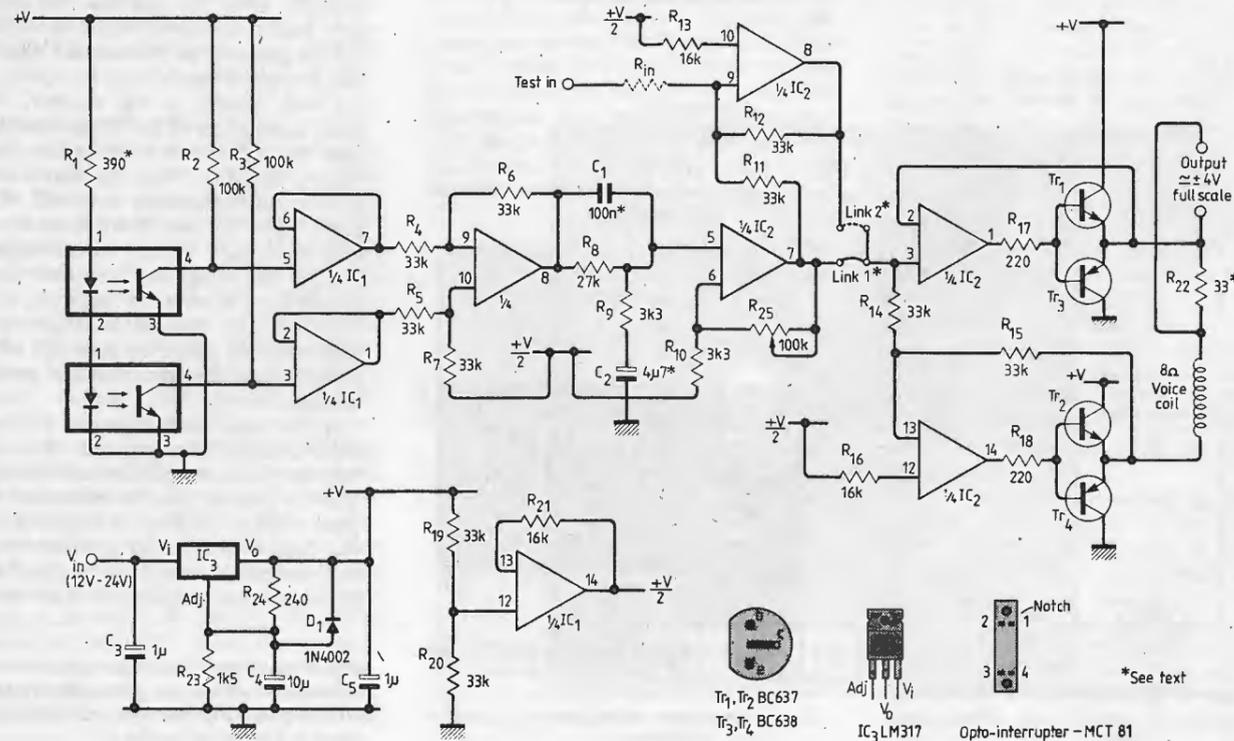


Fig. 4. Loudspeaker unit is prepared by separating the voice-coil from the magnet and cutting away the paper cone.

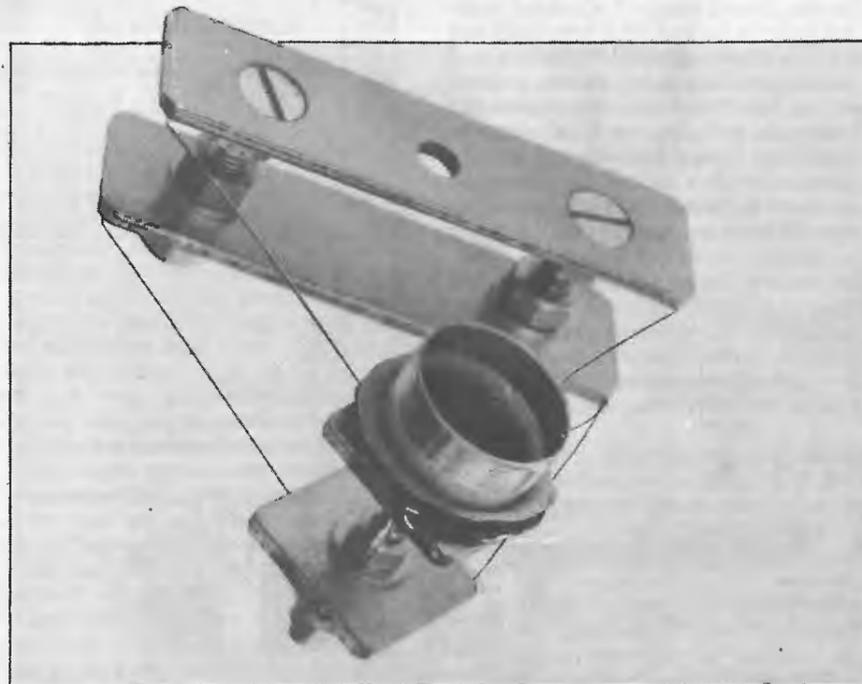


Fig. 5. Flexure assembly, showing voice-coil on top.

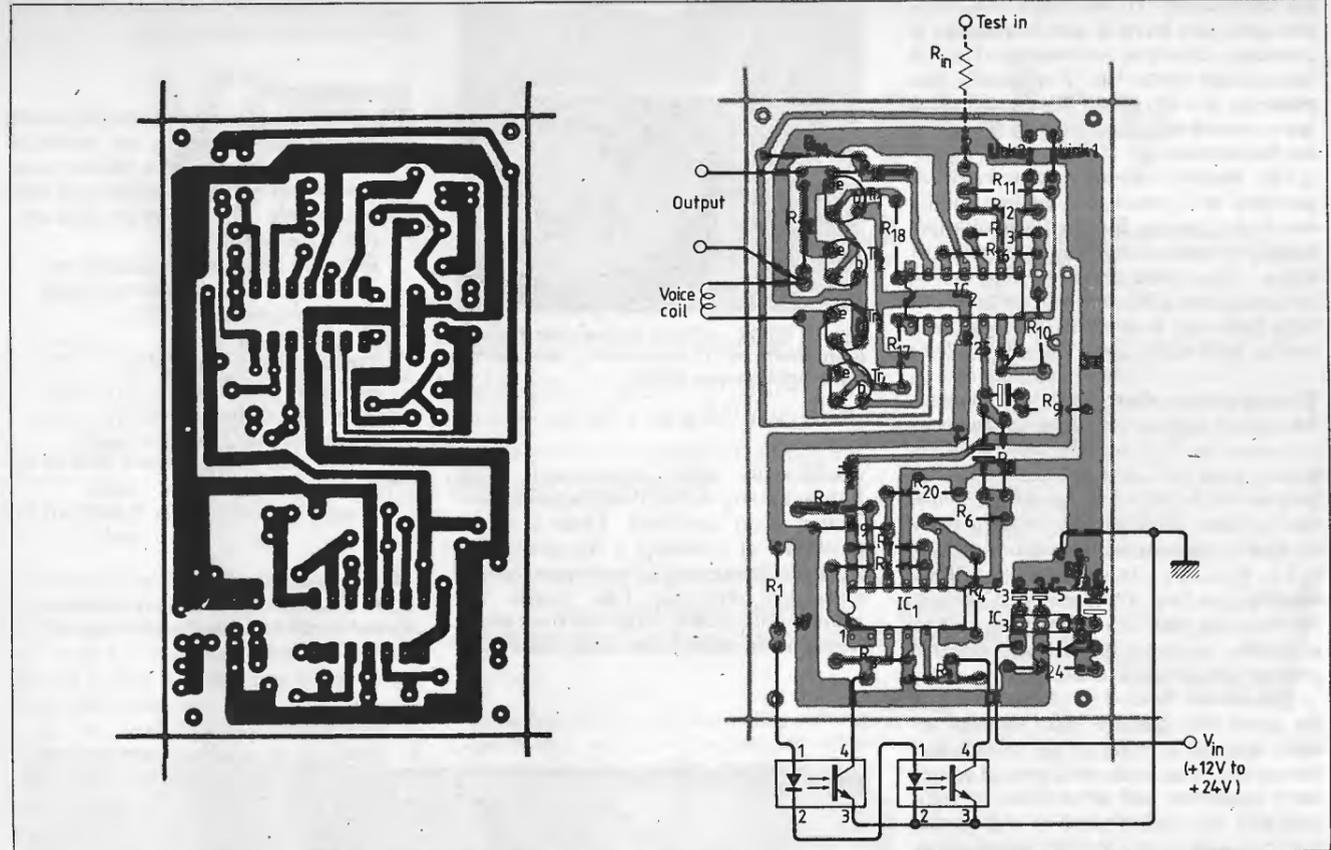


Fig. 7. Circuit-board pattern for servo-amplifier, viewed from track side.

Fig. 8. Component layout for servo-amplifier.

floating and not referenced to ground; a floating meter or a differential amplifier must therefore be used to measure this voltage.

Since the opto-interrupters have widely varying current gains it is necessary to select the value of  $R_1$  for the specific components used. To do this connect the opto-interrupters as shown in Fig. 6 before mounting them on the transducer. With the optical path of the sensors unobstructed, find the maximum value of  $R_1$  for which the output voltage on pin 4 of the less sensitive of the two sensors is less than 0.3V (measured with a meter with an input impedance of at least 1M $\Omega$ ). The value of  $R_1$  found in this way is the appropriate one to use. The output voltage of the more sensitive sensor will be lower than the less sensitive one. To avoid damage to the sensors  $R_1$  should not be less than 200 $\Omega$ . The sensor with the higher gain should be used as the temperature compensator and the one with the lower gain, and therefore the greater linear range of operation, for the moving mass position sensor.

When  $R_1$  has been selected the two sensors can be mounted on the transducer and connected to the servo-amplifier. The cut-off of the temperature compensation sensor should be adjusted so that the voltage on pin 4 is near 4V. The height of the position sensor above the base-board can then be adjusted so the voltage on pin 4 is approximately 4V at mid-travel of the moving mass.

With  $R_{25}$  set to zero, connect the voice-coil and then slowly increase  $R_{25}$ . If the mass moves to either stop and stays there, the sign of the feedback is incorrect and the voice-coil connections must be reversed. If all is well the mass will assume a

stable position between the two stops. As  $R_{25}$  is further increased the moving mass will probably start to oscillate, emitting an audible tone at 100 to 200Hz.  $R_{25}$  should then be reduced until the oscillation just ceases and then approximately halved in value. If necessary the height of the position sensor can be adjusted to centre the moving mass between its stops. If the arrangement of the transducer is similar to the one described this procedure should produce a system with good stability and performance. If the design is altered significantly the compensation network may require changing.

The prototype transducer had a full scale range of  $\pm 2G$ , or  $\pm 0.1$  newton ( $\pm 0.021b$ ) when used to measure forces. This range was selected so that accelerations of  $\pm 1G$  could be measured while allowing reasonable headroom to accommodate the electrical damping introduced by the phase-lead network. To increase the transducer range  $R_{22}$  should be reduced, taking care not to exceed the voice-coil dissipation limit. To reduce the transducer range  $R_{22}$  can be increased or the moving mass increased in size.

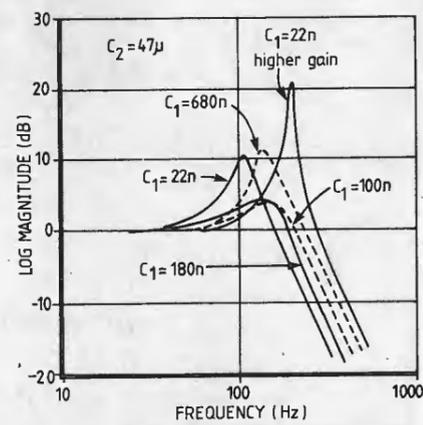


Fig. 9. Altering the value of the lead-compensation capacitors affects the stability and frequency-response of the system.

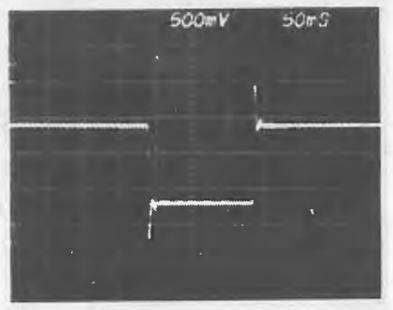


Fig. 10. Step-response of the system with  $C_1 = 180nF$ . A degree of overshoot is visible.

low frequencies. To overcome this problem some gain boost at low frequencies is provided, inevitably accompanied by a destabilizing phase-lag. Fortunately this phase-lag is not critical since the system has a considerable margin of stability at low frequencies.

The desired lead-lag compensation is provided by  $C_1$  and  $R_8$  for the lead and  $C_2$  and  $R_9$  for the lag. Two methods of arriving at appropriate compensation networks will be described, the first of which is suitable for constructors without access to test equipment. Leaving  $R_8$  and  $R_9$  at their normal values set  $C_1$  to a low value (22nF) to provide some minimal damping and  $C_2$  to a large value (47 $\mu$ F) so the lag compensation only has effect at very low frequencies. Increase  $R_{25}$  until audible oscillation occurs, or if it fails to do so increase the gain further by reducing  $R_{10}$ . When oscillation occurs determine its frequency by comparing the note with a piano. Select  $C_1$  and  $C_2$  such that  $1/2\pi R_8 C_1$  is about half the observed resonant frequency and  $R_9 C_2$  is between six and ten times  $R_8 C_1$ . Then adjust  $R_{25}$  to about half the value which produces the onset of oscillation.

The second method of compensation is for those who desire a more detailed insight into the stability of the system and have access to an audio oscillator or square wave generator and an oscilloscope. To optimize the performance of a feedback system it is necessary to apply sinusoidal or step inputs and observe the system response. A summing amplifier has been provided which can be inserted before the power stage by removing link 1 and inserting link 2 (Fig. 6). Since this amplifier inverts, the connections to the voice coil must be reversed when it is in circuit. Any signal (Test in) applied to this amplifier through a suitable resistor ( $R_{in}$ ) will force a current in the voice coil which will have an identical effect to an applied acceleration. Under these circumstances the voltage 'Test in' can be regarded as an input acceleration, and the system output effectively appears at pin 7 of IC<sub>2</sub>. With the aid of an oscillator and an a.c. voltmeter or oscilloscope it is possible to measure the system frequency response. To examine the step response of the system, a square-wave generator and oscilloscope are needed. Frequency response measurements carried out on the prototype system with various values of lead-compensation capacitor  $C_1$  are plotted in Fig. 9. For comparison the step response for two of the cases shown in Fig. 9 are reproduced in Fig. 10 and Fig. 11. The aim is to select a value for  $C_1$  which produces an acceptable response overshoot at the highest possible frequency. When changing  $C_1$  it will be necessary to vary  $R_{25}$ , remembering that increasing gain increases the resonant frequency and reduces the effective damping of the resonance. When a suitable value of  $C_1$  has been determined,  $C_2$  (which should have been initially set to a large value) should be reduced until the measured response just starts to deteriorate. The effect of large excursions of the moving mass should be checked by deflecting it to one of its stops and then releasing it. This is necessary because it is possible to have a

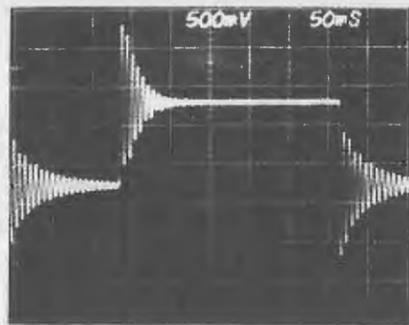


Fig. 11. With  $C_1=680nF$  the servo is grossly under-damped. The value of  $C_1$  selected for the prototype was 100nF.

conditionally stable arrangement which bursts into stop-to-stop low frequency oscillation when disturbed. There is also a possibility of instability if the mechanical resonant frequency of any part of the transducer structure falls within the operating frequency range. All these problems can be sorted out with the aid of

## DESIGN COMPETITION

This is the third month of our competition 'Design an electronic device to help the disabled'. Already, registrations are coming in, and the competition seems certain to bring out some extremely useful equipment to enable physically handicapped people to lead a more independent and fuller life.

This is a worthwhile spare-time activity. The prizes are attractive and the outcome could be more than just a clever design exercise: it could be the means of assisting someone to speak, read, move about or even 'see'.

The rules are set out on page 88: they are few and quite simple. All you need to do in the first place is to register with WW your intention to enter the competition. Think about it — but not for too long, because time is running out.

careful measurements, time, and a good book on control system theory. **WW**

### Performance

The following performance measurements have been carried out on two prototype transducers using precision masses to apply forces and a digital voltmeter to measure the output. The results obtained are:

Full scale output  $\pm 4V$   
Full scale input  $\pm 2G$ , acceleration  
 $\pm 0.1$  newton, force

Resonant frequency 150Hz  
Damping ratio  $\approx 0.3$   
Linearity better than 0.1%  
Zero drift  $\approx 0.01\%/^{\circ}C$   
Sensitivity drift  $< 0.01\%/^{\circ}C$   
Resolution (set by output noise)  
with d.c.-100Hz filter 0.03% of full scale  
with d.c.-10Hz filter 0.003% of full scale

### Background reading

H. K. P. Neubert, Instrument Transducers. Oxford at the Clarendon Press 1963, pp.363-381.

# Viewdata display module

Colour text and graphics in 'level one' teletext format are provided and the display is controlled by either a serial or parallel link from the host computer. With the addition of a modem, the display module can be programmed to display data directly from a viewdata computer.



by Dennis N. Pim

Information received by the display module can be divided into two categories: the first is data transferred directly to one of the rams for immediate display, and the second is data decoded as a command to the display processor.

As the module is software-controlled there is great flexibility in its mode of operation. For this reason the following descriptions of the commands available and software required only apply to my prototype where the module was designed to be connected to a host computer and receive/send data serially at 4800baud. This should demonstrate the capabilities of the module and provide sufficient detail for it to be adapted to other applications.

In the prototype therefore when a data word is received from the host computer, its most significant bit is examined. If it is logic one then the data is treated as a command, if it is logic zero the data is stored directly in the current cursor location of the currently addressed store (which is not necessarily the one being displayed at that instant), and the cursor is moved to the next location in the store. Thus ordinary strings of characters for display (including teletext control commands such as colour/graphics controls) can be sent to the module without intervening commands and will be stored correctly, ready for display.

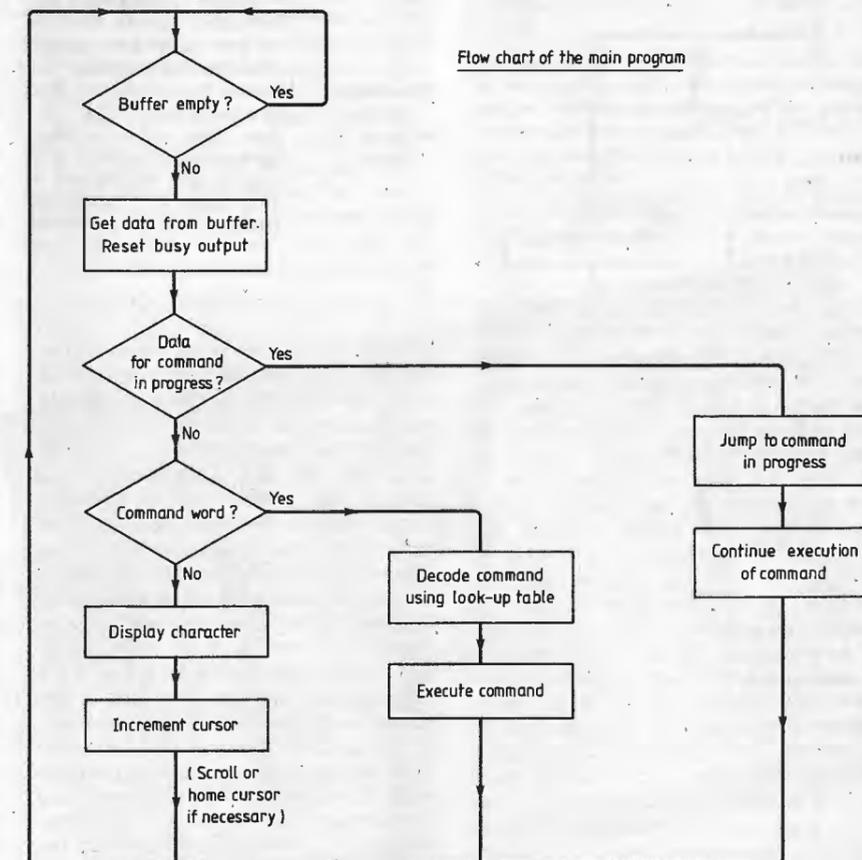
For commands (most significant bit=1) the first five bits of the data are decoded with the aid of a look-up table, and the particular command is then executed. This gives 32 possible commands some of which use the two remaining spare bits of the data word (bits 5 and 6) to provide variations in the particular command.

To preserve compatibility with the codes used in viewdata transmissions, commands such as carriage return and line feed have their usual ASCII codes (only the most significant bit, 7, is set to 1 to indicate a command). Table 1 lists the commands implemented in the prototype. The software required for these fits neatly into the 1K of program rom available in the 8048 processor. Notice that some of the commands require a second or third data word from the host processor before the command can be executed. Notice also that some commands produce output data

to be sent to the host computer, although the module will never output data unless instructed to do so. The commands shown demonstrate the sort of functions that can be performed within the display module to reduce the need of the host computer from having to perform some of the more common display processes.

For specific applications, there are many other display functions that could be implemented in the display module, such as a simple block move routine. This is of course at the expense of some of the other

Photograph shows display module described in April and May issues together with ViCom experimental videotex computer by Deaconhouse Ltd. In its teletext application GIM decoder chip AY-3-7910 is added to the display module. Telesoftware can then be captured into one of the page stores and "dumped" using command 28 to the host computer for execution/processing. The display module is suitable for the 'level one' standard of Prestel, but other display standards can be catered for by changing the display module as appropriate chips become available.



commands as only 1K of program rom is available.

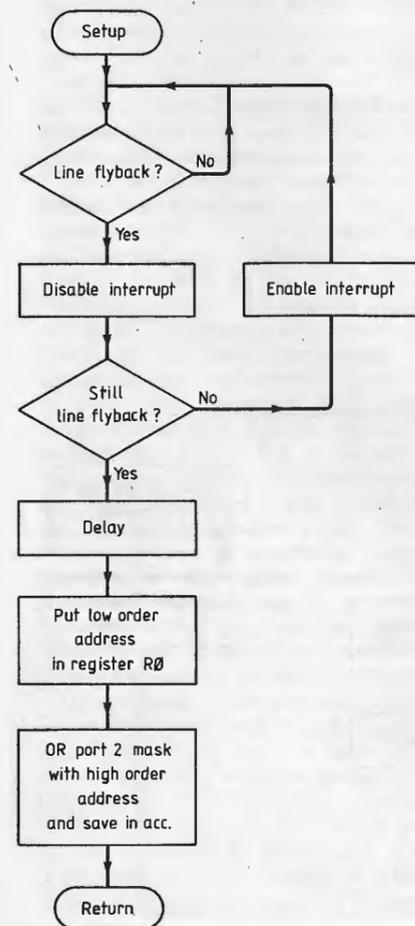
### Software

It would not be instructive to provide a complete assembly language listing of the program as it stands in the prototype; not only is it very lengthy and it contains many complicated programming tricks to reduce the memory requirement to fit into the 1K of program rom available, but it has also been specifically developed to meet my requirements. The software must be tailored to each individual application. However, it is worth explaining the subroutines which access the display rams and send commands to the video generator, as these would be required in any implementation of the display module. A knowledge of 8048 assembly language is assumed in the explanation of these routines.

Firstly though, consider the overall structure of the whole program, see flow-chart. When idling, the processor continually looks at the input buffer waiting for commands or display data. This buffer, consisting of 24 of the ram locations within the 8048, is supplied with data as it arrives from the host processor by the interrupt routine which decodes the serial/parallel data and stores it in the next free buffer location. (Software decodes the serial data stream.)

When the main program detects that a new data word is available it is loaded from

SETUP subroutine



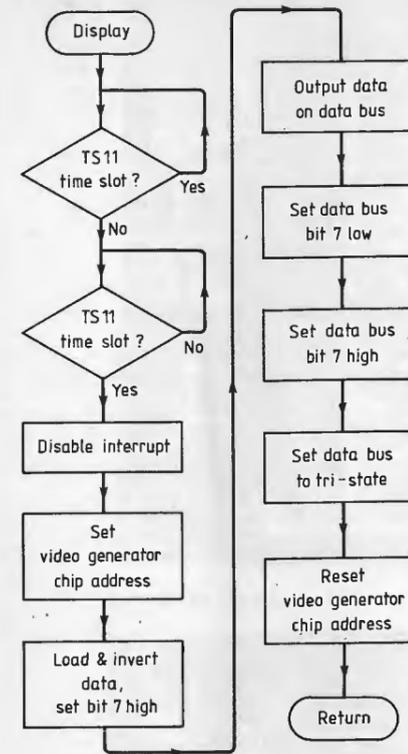
Command	Function	Function
0 Send status	The flag status register in the display module is transmitted. Eight bits interpreted as 0 - scrolling on/off, 1 - scrolling down/up, 2 & 3 - currently addressed store, 4 - cursor on/off, 5 - reveal/conceal control codes at the cursor position <sup>1</sup> , 6 & 7 - currently-displayed store.	15 Set display controls
1 Scroll	Currently-addressed store scrolled (if scrolling is on).	16 Set scrolling
2 Reset	Display module reset and screen cleared.	17 Cursor on
3 Read display address	Current cursor row and column position transmitted.	18 No action.
4 Read display memory	Character at cursor position in currently-addressed store transmitted.	19 No action.
5 Write to display memory	Next data word received stored at the current/cursor position (cursor not incremented).	20 Cursor off
6 Read port	Current state of parallel port (port 1 in the 8048) transmitted.	21 No action.
7 Write port	Next data word received used to set 8 bits of parallel port (serial input only).	22 Set reveal
8 Backspace	Cursor moved one location backwards <sup>2</sup> .	23 No action.
9 Cursor forward	Cursor moved one location forward <sup>2</sup> .	24 Cancel
10 Cursor down	Cursor moved one row downwards <sup>2</sup> .	25 No action.
11 Cursor up	Cursor moved one row upward <sup>2</sup> .	26 No action.
12 Clear screen	Two variations: - whole screen cleared and cursor homed - screen cleared from and including cursor position to end of screen (cursor position unchanged).	27 No action.
13 Carriage return	Cursor moved to the start of current row.	28 Dump
14 Select store	Next data word received determines new store to be addressed, displayed or addressed and displayed. Options determined by settings of bits 5 & 6 in command word.	29 No action.
		30 Cursor home
		31 Set cursor

the buffer. If this data is not the second or third byte of a multiple byte command, in which case execution of the command in progress continues using the new data received, its most significant bit is tested. If this is zero, the data is assumed to be a character for display and is therefore directly stored at the cursor position in the currently-addressed page store. The cursor position is then incremented by one, which may involve homing the cursor or scrolling the display if the cursor was positioned in column 40 of row 24. If the most significant bit of the data word is set to one, it is a command and the first five bits of this word are used in a look-up table to transfer processing to the required command execution routine. After execution of the command, or displaying the character and incrementing the cursor as necessary, processing is returned to the start of the main program again.

Apart from the scrolling operation, and the clear page function (which requires at least one video frame of 20ms), most of the commands and data display are executed within 800µs. This time is less than the stop bit time of serial data at 1200baud so the module can directly display data from a viewdata computer if required.

I didn't specifically consider the execution time of the program during development and it seems likely that the 800µs time could be reduced by careful program design. There is, however, some unavoidable time wastage of up to 64µs (the time for one video line) each time the processor has to access the display memories. This occurs three times each time a character is stored, once to store the character and clear the cursor bit, once to read the data at the new cursor position, and once to add the cursor bit at this new location without altering the character

DISP subroutine



stored there. However, I am working on a version which combines the last two operations into one line-flyback interval.

In any implementation of the display module, the subroutines to read and write to the page stores during line flyback, and the subroutine to send commands to the video generator will be required. So the operation of these is described next; refer to assembly language subroutine illustration.

The setup subroutine performs two functions. Firstly, it finds the next line sync pulse and secondly it sets up the various registers required for the read or write operations. The timing of this subroutine is carefully arranged so that the next line flyback interval (56µs after the start of the previous line sync pulse, the time at which the video generator frees the address and data buses) occurs immediately after execution of the RET instruction.

On entry into the subroutine, the current cursor address is held in the two memory locations addressed by the contents of registers R0 and R1 (low-order eight bits addressed by R0). Register R6 contains the port 2 mask so that when the high-order address lines are set up on bits 0 and 1 of port 2, the currently-addressed page bits (port 2 bits 2 & 3) are set up correctly, the address latch output is enabled (port 2 bit 4 is set low) and none of the other bits of port 2 are altered.

The flow chart of the subroutine describes its operation. The second test for the line sync pulse is required in case an interrupt occurred after the first test and before the interrupt was disabled (a time window of about 5µs). If this happens the interrupt is enabled again and the processor waits for the next line sync pulse after servicing the interrupt. For the processor

### Components

IC<sub>1</sub> 8048 microcomputer (8748 eeprom version)  
 IC<sub>2</sub> 74LS123  
 IC<sub>3</sub> 74LS373  
 IC<sub>4</sub>, IC<sub>5</sub> 2K×8 static ram (e.g. Fujitsu MB8416)  
 IC<sub>6</sub> 74LS125  
 IC<sub>7</sub> 74LS04  
 IC<sub>8</sub> 9735 video generator\*  
 D 1N4148  
 R<sub>1</sub>, R<sub>2</sub> 1kΩ all 5%, ¼ watt  
 R<sub>3</sub> 27kΩ  
 R<sub>4</sub>, R<sub>5</sub> 1kΩ  
 R<sub>6</sub>, R<sub>7</sub> 10kΩ  
 R<sub>8</sub>, R<sub>9</sub> 10kΩ  
 R<sub>10</sub> to R<sub>12</sub> 22kΩ

R<sub>13</sub> 10kΩ  
 R<sub>14</sub> 4.7kΩ  
 R<sub>15</sub> 10kΩ  
 R<sub>16</sub> 22kΩ  
 R<sub>17</sub> to R<sub>19</sub> 100Ω†  
 R<sub>20</sub> 10kΩ  
 R<sub>21</sub> 330Ω  
 R<sub>22</sub> 100Ω†  
 C<sub>1</sub> 0.1µF  
 C<sub>2</sub> 1µF 10V electrolytic  
 C<sub>3</sub> 220pF  
 C<sub>4</sub> 1nF  
 C<sub>5</sub> to C<sub>9</sub> 0.1µF

\* GIM tell us they are unable to supply the video generator i.c. An equivalent device, type MR9735, should be available through Plessey distributors or from Deaconhouse.  
 † Incorrectly labelled in circuit diagram.

to execute past the second line sync test, the pulse must be 10µs wide, set by the monostable timing components R<sub>3</sub> and C<sub>4</sub>.

If the host processor starts to send a data word during a read or write operation there may be up to 64µs delay before the 8048 responds, as the interrupt has to be disabled. This won't affect the correct decoding of data at 4800 baud or less and the possibility has been accounted for in the arrangement of the sampling points of the decoding software. Alternatively, for faster rates, or parallel input, the data output line (port 2 bit 7) can be set low during a read or write operation to indicate that the 8048 is busy and cannot accept a new data word.

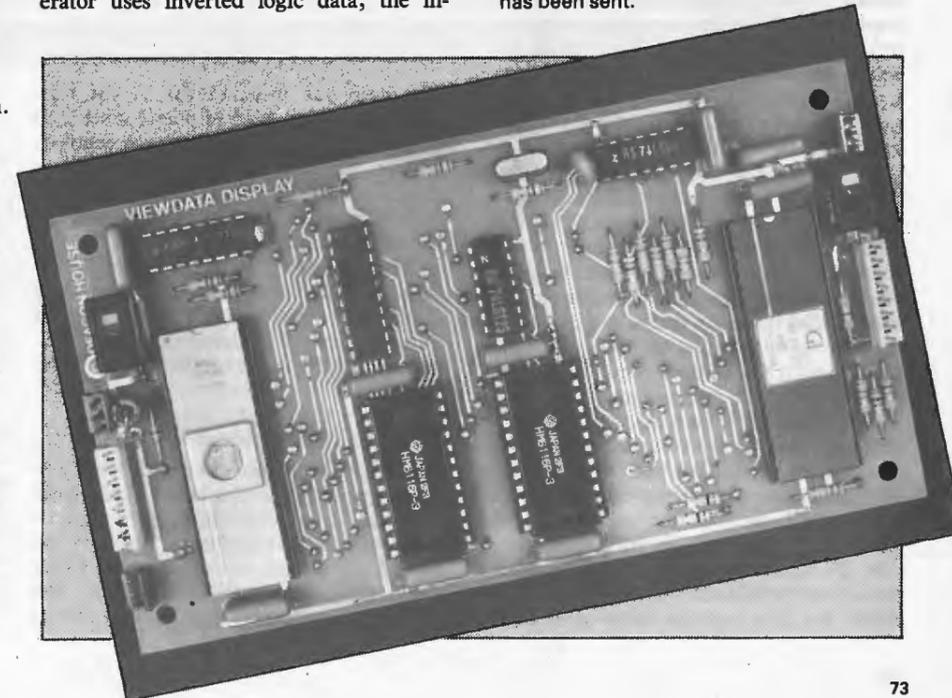
Operation of the read and write subroutines is comparatively straightforward. After calling the setup subroutine, the read subroutine sets the address, page and address latch output enable outputs on port 2 (data and address buses are now free) and uses an external move instruction (MOVX) to read the currently-addressed display ram (the low-order display address held in R0 is automatically latched in IC<sub>3</sub> during execution of the MOVX instruction). Bits 0 to 4 of port 2 are then set to their high impedance state again so that the video generator can have access to the data and address buses again. The resulting data is then inverted, as the video generator uses inverted logic data, the in-

Table 2. Video generator command words - see AY-3-9735 data sheet for full list.

Display function	Hex value
PICTURE ON & PAGE 0	C8
TEXT & SYNC ON	D1
(These commands should be sent in this order on power-up)	
CURSOR ON	A1, B1*
CURSOR OFF	A1, B4*
CLEAR ADDRESSED PAGE	94†
HALF-PAGE EXPANSION	D3
(Cycles top, full, bottom, full etc)	
DISPLAY FUNCTION REVEAL/CONCEAL	HEX VALUE D2
MIX mode	E2
ROUNDING (in interface mode) & FLASHING OFF (for printing etc)	D9
SELECT DISPLAYED	C0 to C3
PAGE	(page 0 to 3)
SELECT ADDRESSED	80 to 83
PAGE	(page 0 to 3)

\* These two command words must be sent in the given order in the same TS11 time slot (the DISP subroutine has a second entry point which bypasses the TS11 tests so that the second word can be sent in the same time slot).

† The display rams should not be accessed for one video frame after this command has been sent.



```

*****
;
; READ SUBROUTINE
;
; READS ONE CHARACTER FROM
; THE CURRENTLY ADDRESSED
; DISPLAY RAM
;
; ON ENTRY - (R0)=CURSOR ADDRESS LOW
;           - (R1)=CURSOR ADDRESS HIGH
;           - (R6)=PORT 2 MASK
;
; ON EXIT - (A)=CHARACTER READ FROM RAM
;
*****
READ: CALL SETUP ;FIND LINE SYNC EDGE &
;SET UP ADDRESS REGISTERS
;SET ADDRESS HIGH, PAGE SELECT
;OUTPUTS & ENABLE ADDRESS LATCH
;OUTPUTS
MOVX A,@R0 ;READ DISPLAY RAM
ORL P2,#1FH ;RESET PORT 2 OUTPUTS
EN I ;ENABLE INTERRUPT (INTERRUPT
;DISABLED IN SETUP)
RET ;RETURN
;
; WRITE SUBROUTINE
;
; STORES ONE CHARACTER AT THE
; CURSOR POSITION IN THE CURRENTLY
; ADDRESSED DISPLAY RAM
;
; ON ENTRY - (R0)=CURSOR ADDRESS LOW
;           - (R1)=CURSOR ADDRESS HIGH
;           - (A) =CHARACTER FOR DISPLAY
;           - (R6)=PORT 2 MASK
;
*****
WRITE: CPL A ;INVERT DATA FOR VIDEO
;GENERATOR
MOV A,R3 ;SAVE CHARACTER IN R3
CALL SETUP ;FIND LINE SYNC EDGE &
;SET UP ADDRESS REGISTERS
;SET ADDRESS HIGH, PAGE SELECT
;OUTPUTS AND ENABLE ADDRESS LATCH
;OUTPUTS
MOV A,R3 ;LOAD CHARACTER FROM R3
MOVX @R0,A ;STORE CHARACTER IN DISPLAY RAM
ORL P2,#1FH ;RESET PORT 2 OUTPUTS
EN I ;ENABLE INTERRUPT (INTERRUPT
;DISABLED IN SETUP)
RET ;RETURN

```

Deaconhouse Ltd, of 57 Guildford Street, Chertsey, Surrey (tel 09328 66015) say they will supply the 85 x 155mm double-sided printed board shown opposite.

Interrupt is enabled, and the subroutine returns.

The write subroutine operates in a similar fashion except the character to be displayed (held in the accumulator on entry) is inverted and stored in register R3 before execution of the setup subroutine. It is then loaded into the accumulator again just before execution of the MOVX instruction to store the character.

The subroutine to send commands to the video generator, called DISP, operates as follows; the first two instructions find the rising edge of the 8048 T1 input - this represents the start of the TS11 time slot when the video generator can receive commands. The interrupt is disabled and bit 5 of port 2 is set low to complete the 1111XX0XXXX address required for the video generator to respond to a command. The command data to be sent to the video generator, held in the accumulator, is then inverted for the DATA bus of the display chip. The most significant bit which acts as a strobe is set high and the data placed on the bus by the OUTL BUS,A instruction. The most significant data bit is then pulsed low (minimum pulse width 4µs) to strobe the data into the video generator.

```

*****
;
; SETUP SUBROUTINE
;
; FINDS THE NEXT LINE SYNC
; PULSE AND SETS THE CURSOR
; ADDRESS LOW IN R0, THE
; CURSOR ADDRESS HIGH AND
; CURRENTLY ADDRESSED PAGE
; IN ACCUMULATOR AND RETURNS
; AT THE START OF THE NEXT
; LINE FLYBACK INTERVAL
;
*****
SETUP1: EN I ;ENABLE INTERRUPT AGAIN
;SETUP ;WAIT UNTIL NEXT LINE
;SYNC PULSE
DIS I ;DISABLE INTERRUPT
SETUP2: JTO SETUP1 ;JUMP IF LINE SYNC
;PULSE NOT STILL THERE
MOV A,#3 ;SET DELAY
DEC A ;DECREMENT ACCUMULATOR
JNZ SETUP3 ;JUMP UNTIL (A)=0
MOV A,@R0 ;LOAD CURSOR ADDRESS LOW
MOV R0,A ;SAVE IN R0
MOV A,R6 ;LOAD PORT 2 MASK
ORL A,@R1 ;ADD CURSOR ADDRESS HIGH
RET ;RETURN
;
; SUBROUTINE DISP
;
; SENDS A DISPLAY COMMAND TO THE
; VIDEO GENERATOR
;
; ON ENTRY - (A)=COMMAND CODE TO BE SENT
;
; ENTRY POINT "DISP2" ALLOWS A
; COMMAND TO BE SENT DIRECTLY
; WITHOUT WAITING FOR THE NEXT
; TS11 TIME SLOT - USED FOR
; CURSOR ON/OFF COMMANDS
;
*****
DISP: JT1 DISP ;WAIT UNTIL NOT TS11
;TIME SLOT
DISP1: JNT1 DISP1 ;WAIT UNTIL START OF
;NEXT TS11 TIME SLOT
DISP2: DIS I ;DISABLE INTERRUPT
;ANL P2,#0DFH ;SET VIDEO GENERATOR
;ADDRESS OUTPUT
; (PORT 2 BIT 5 LOW)
CPL A ;INVERT COMMAND CODE
;FOR VIDEO GENERATOR
ORL A,#80H ;SET BIT 7 HIGH
OUTL BUS,A ;SET COMMAND ON DATA BUS
ANL A,#07FH ;SET BIT 7 LOW
OUTL BUS,A ;SET STROBE BIT LOW ON DATA BUS
ORL A,#80H ;RESET BIT 7 HIGH
OUTL BUS,A ;SET STROBE BIT HIGH ON DATA BUS
ORL A,#0FFH ;SET ALL BITS HIGH
OUTL BUS,A ;SET DATA BUS TO TRI-STATE AGAIN
ORL A,#20H ;RESET VIDEO GENERATOR
;ADDRESS OUTPUT
EN I ;ENABLE INTERRUPT
RET ;RETURN

```

The data bus then returns to the high impedance state, bit 5 of port 2 is set high impedance again, the interrupt is enabled, and the subroutine returns. Table 2 shows the hex values of the command data required by the video generator to achieve the various display facilities.

These three subroutines are the only ones that would have to be used in any application of the display module. The rest of the program is determined by the application and the functions required of the module.

#### Constructional notes

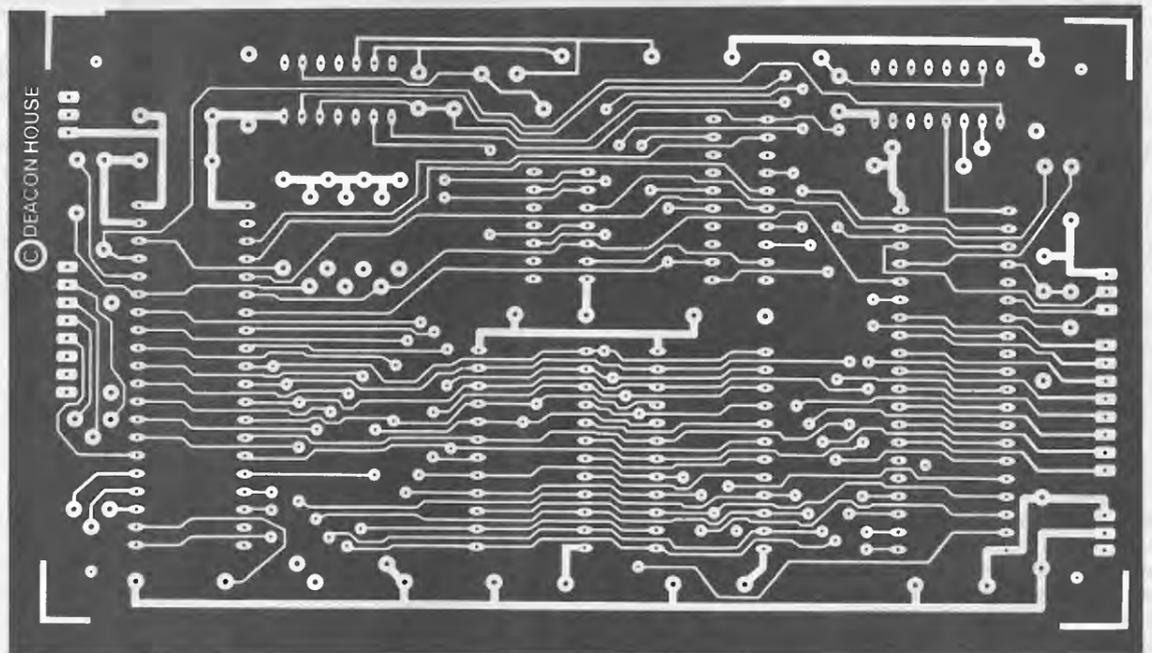
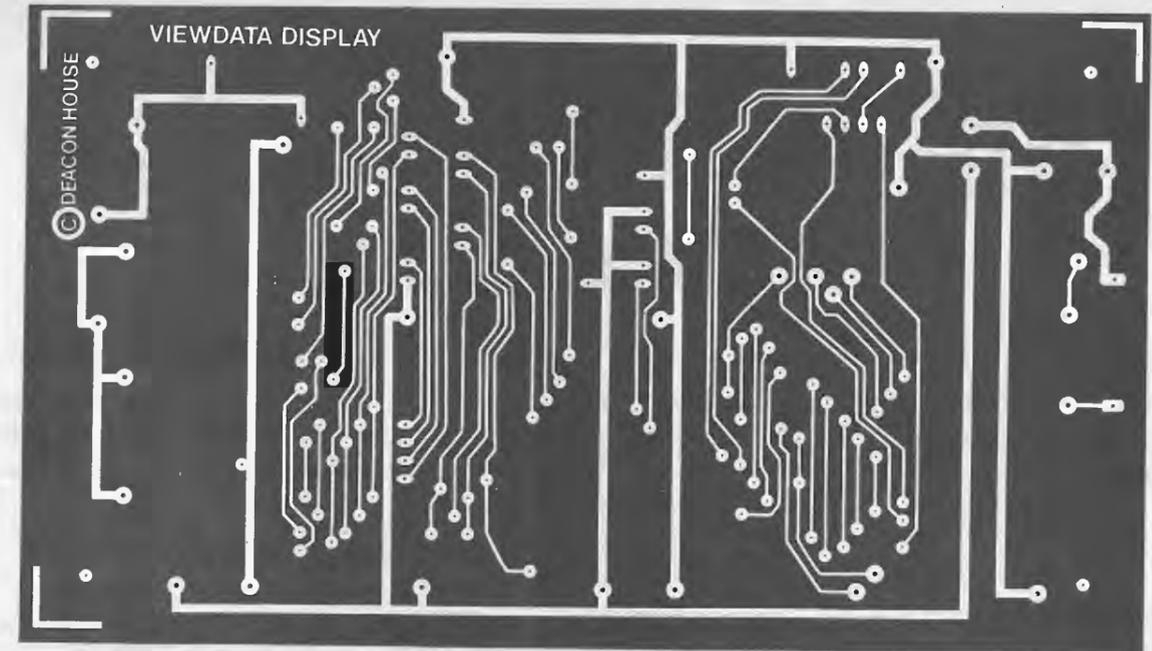
The original was constructed on a half-Eurocard prototype wiring board. Apart from the usual considerations as to the placement of the decoupling capacitors no special precautions were taken with either the component or the wiring layouts. The only hardware problem met so far is that

the video generator i.e. sometimes does not power-up correctly. On the software side, I recently used different versions of the display generator - one which automatically displays the cursor when initially set to the text mode and one which does not. Both problems appear to stem from the use of pre-production prototype display generators, and I do not envisage these occurring with production i.cs.

#### Stand-alone viewdata decoder

The following notes are intended as a guide to those who wish to use the module to directly decode the 1200baud serial data arriving from a viewdata computer. I have not tried these modifications.

The first consideration is whether the module can be constructed and programmed to transmit 75baud data to the viewdata computer as well as receive the



1200baud data. It is possible to connect a keyboard with a parallel ASCII output to the parallel port on the module, and use the data out line (port 2, bit 7) as the 75baud data line. The most significant bit of the parallel port could be used as a keyboard strobe (the strobe pulse width should be arranged to be less than the transmit time of one 75baud character, but longer than the transmit time of one 1200baud character, i.e. between about 10ms and 100ms. This ensures that the strobe will be recognised even if it occurs whilst a character is being received). The problem with this method is that if a character is received whilst one is being transmitted, the transmitted character will be corrupted because the processor will be interrupted by the incoming character. To ensure full duplex operation therefore, it

may be wiser to employ a separate uart to generate the 75baud signal.

On the software side, the following changes would have to be made.

- Change the software delays in the interrupt routine to decode 1200 baud data rather than 4800.
- Change the serial transmit routine delays to send 75baud data (if port 1 is used to connect the keyboard).
- Perform a parity check on the incoming data using the most significant bit and display the parity error character (7F hex) if an error occurs.
- Change the command look-up table to perform only the required viewdata cursor controls (such as back space, carriage return, clear screen, etc).
- Set a flag on receipt of an ESC code.

- If the ESC flag is set convert the next received character (if it is between 40 hex and 60 hex) to a teletext control code (clear bit 7 of the character) and display it, or ignore it if it is not in the above range. The ESC flag is then cleared.
- On receipt of the ENQ character (05 hex) to send the required log-on data (which should be programmed into the 8748 rom).

To have enough program space to incorporate these changes would require the deletion of some of the editing facilities described in Table 1, such as scrolling, part clear, or dump.

A modem would of course be required in any stand-alone application of the display module to transmit/receive the correct f.s.k. signals.

# Digital filter design procedure

These examples of the design of a simple digital filter and, in contrast, that of a digital version of a fourth-order Butterworth filter, show how laborious mathematics may be simplified and the "recurrence formula" for the filter written without having to solve a fourth order equation.

Many digital filters can be designed simply on their own merits. But in the case of the digital equivalent of an analogue filter, such as the Butterworth filter, the situation is complicated by the need to use a bilinear transformation, resulting in laborious algebra. This can be largely avoided for a fourth-order filter by following this procedure, substituting cut-off and sampling frequency values, and by using the tabular form suggested.

The end product of filter design procedure is the recurrence formula in a form which can readily be entered into the computer or micro processor program that constitutes the filter. In addition it is desirable to plot the  $j\omega$  frequency spectrum in terms of the sampling frequency to check that the filter has the desired characteristics.

Two starting points are considered:

- where the z-transfer function and hence the z-plane diagram can be formulated from a comparatively simple requirement. The example described is the digital equivalent of a simple tuned circuit.
- where the z-transfer function and the z-plane diagram have to be derived from an analogue filter using a bilinear transformation. The example chosen is

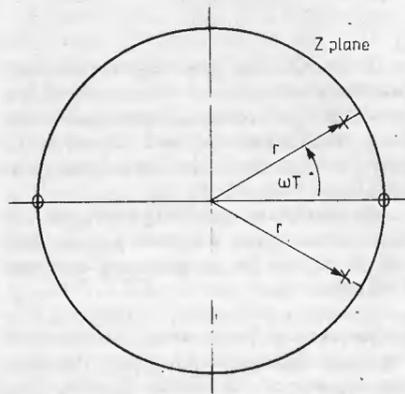


Fig. 1. Z-plane diagram of the digital equivalent of a tuned circuit. Angle represents the resonant frequency and is  $\frac{1}{2}$  of the sampling frequency, which is represented by one revolution round the unit circle.

by J. T. R. Sylvester Bradley

the digital equivalent of a Butterworth low-pass filter.

The two examples are worked in full. In the second example the algebra is laborious and unavoidable but some short cuts are

suggested. It shows that if a digital filter is designed as an equivalent to an analogue filter, coefficients are generated which in most cases require sophisticated arithmetic in the microprocessor. It is often preferable to design a digital filter so that the coefficients can be kept as simple as the hardware requires. (In the Butterworth filter fractional coefficients with a required accuracy of 3 decimal places are unavoidable.)

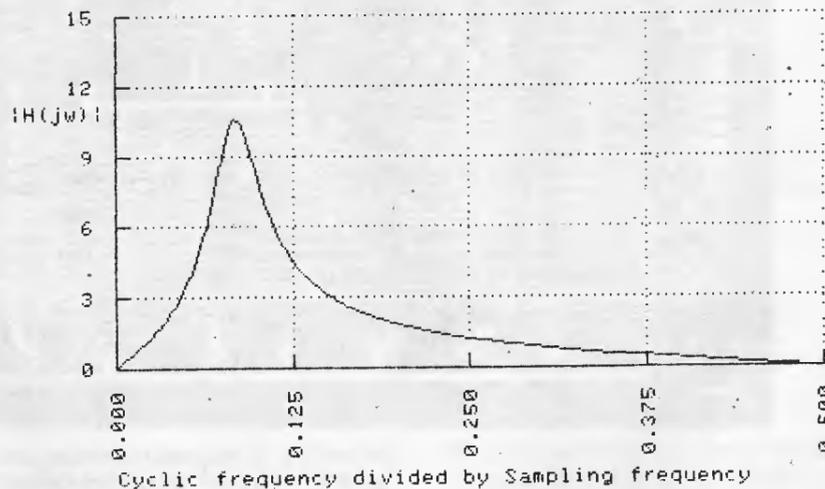


Fig. 2. Response  $|H(j\omega)|$  of the filter in Fig. 1 is plotted against frequency divided by sampling frequency.

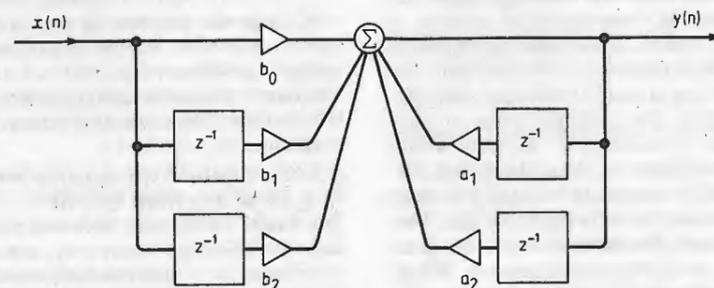


Fig. 3. Realization diagram shows how the microprocessor performs the signal processing. Boxes labelled  $z^{-1}$  are delays of one clock pulse and the small triangles are multipliers (or dividers) by the coefficients shown.  $x(n)$  is the input sample at the instant "now" or "n", and  $y(n)$  is the output sample at the same instant.

Output Values

0  
0  
0  
1  
1.56  
.6236  
-.290784  
-.950739  
-1.2601  
-1.18917  
-.834433  
-.338484  
.147856  
.504827  
.667767  
.632807  
.446287  
.183634  
-.0750228  
-.26578  
-.353848  
-.336721  
-.238668  
-.0995782  
.0379791  
.139906  
.18749  
.179161  
.127624  
.0539729  
-.0191775  
-.0736349

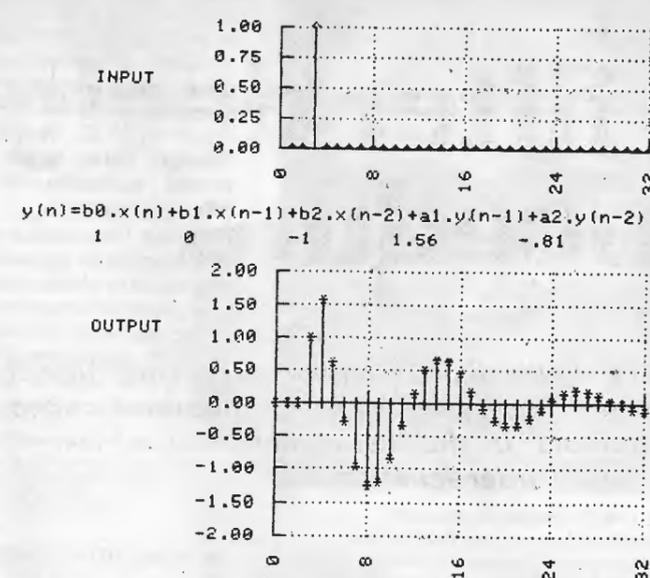


Fig. 4. Input of 32 samples is shown with the corresponding output as (a) a column of values on the left and (b) as a diagram, for the filter whose recurrence formula is shown between the input and output diagrams. A single pulse is shown as the input, resulting in a decaying oscillation at  $\frac{1}{2}$  of the sampling frequency.

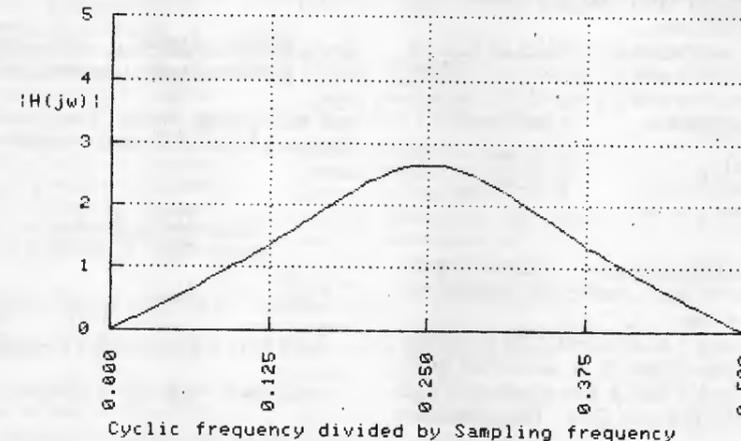


Fig. 7. Flatness or low Q shown in the response curve is a result of choosing very simple arithmetic.

## Method

The process for the design of a digital filter is

- choose a suitable transfer function
- derive the recurrence formula from the transfer function
- write the recurrence formula into the program for the relevant hardware (computer or microprocessor) that will be used to make the filter.

Of these it is the choice of transfer function that causes difficulty. Often a z-plane diagram can be drawn as a step toward the choice of transfer function. In addition a  $j\omega$  frequency spectrum is needed so that one can see whether the filter will meet the requirements of bandwidth and so on; this is derived from the z-plane diagram. In the first, simple case the design almost begins and ends with the z-plane equivalent of an analogue circuit, whereas in the second example, in which a digital version of But-

terworth filter is designed, the z-plane diagram and frequency spectrum are derived from a Butterworth s-plane diagram involving a bilinear transformation, and the algebra is more involved.

The recurrence formula is usefully illustrated as a realization diagram, shown for each example. Finally, in each case the operation of each filter is demonstrated by generating the impulse response using a desk-top computer and a simple Basic program to give input and output signal diagrams.

## Design digital filter equivalent to a parallel tuned circuit

The tuned circuit will have one pole-pair only, at its resonant frequency, and we can assume zeros at zero frequency and at infinity. To be stable, the poles must lie within the unit circle on the z-plane. (In other words the analogue circuit must contain some resistance.) The position of the

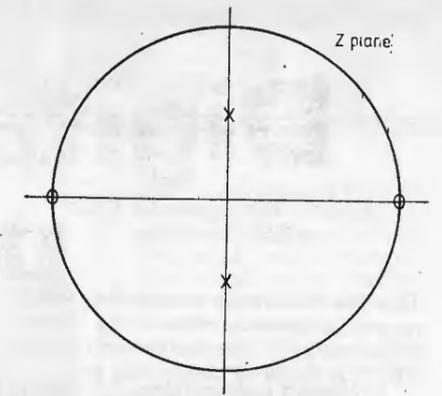


Fig. 5. Z-plane diagram has been chosen with very simple ratios to simplify arithmetic in the microprocessor.

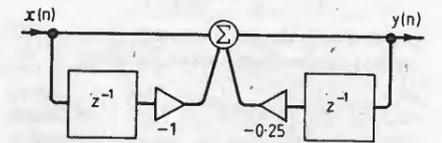


Fig. 6. Realization diagram only contains one multiplier with a coefficient of  $\frac{1}{4}$ , so the arithmetic in the microprocessor is very simple.

poles is dictated by the resonant frequency in relation to the sampling frequency, and to the Q required.

Two examples are worked, one with pole positions chosen arbitrarily with the resonant frequency any value less than half the sampling frequency, and the other with pole positions chosen for arithmetic simplicity with a simple microprocessor in mind (e.g. the MMD1).

## Step 1 - draw the z-plane diagram.

Suppose the sampling frequency has already been chosen as  $12 \times f_0$ , where  $f_0$  is the required resonant frequency of the tuned circuit. The digital filter is designed by locating a pole on the z-plane at an angle of  $\frac{1}{12}$  of a revolution, as one complete revolution of the z phasor represents the sampling frequency. There will automatically be another pole at an angle of  $-\frac{1}{12}$  of a revolution, as the poles come in conjugate pairs. The radius of the poles ( $\exp \sigma T$ ) has been chosen arbitrarily as 0.9 to give an adequately peaky response, without instability. Two zeros are added, at zero frequency and at maximum frequency ( $\frac{1}{2}$  the sampling frequency) to correspond with zeros at zero frequency and infinite frequency for the analogue circuit, Fig. 1. The  $j\omega$  spectrum or cyclic frequency response  $|H(j\omega)|$  is found directly from the z-plane diagram and is shown in Fig. 2.

Because the transfer function  $H(z)$  is zero when  $z = +1$  or  $-1$  (the zeros) and is infinite where  $z = r \cdot \exp j\omega T$  (the poles), the transfer function can be written down directly as

$$H(z) = \frac{(z+1)(z-1)}{(z-r \exp j\omega T)(z-r \exp -j\omega T)}$$

**Step 2 - find the recurrence formula.**

$$H(z) = \frac{Y(z)}{X(z)} = \frac{z^2 - 1}{z^2 - 2r z \cos \omega T + r^2}$$

$$\therefore Y(z) \cdot z^2 - Y(z) \cdot 2r z \cos \omega T + Y(z) \cdot r^2 = X(z) \cdot z^2 - X(z)$$

This can be directly transformed to the recurrence formula, since if the present output sample is  $y(n)$  then the next sample  $y(n+1)$  is found by multiplying by  $z$  (one clock pulse), and the previous sample  $y(n-1)$  by dividing by  $z$ . Thus

$$\begin{aligned} Y(z) & \cdot z & y(n+1) \\ Y(z) \cdot z^2 & y(n+2) \\ Y(z) \cdot z^{-1} & y(n-1) \end{aligned}$$

and so on. So the equation becomes

$$y(n+2) - 2r \cos \omega T \cdot y(n+1) + r^2 \cdot y(n) = z(n+2) - x(n)$$

The present output sample  $y(n)$  in terms of present and previous input samples,  $x(n)$ ,  $x(n-1)$  etc can be found by dividing  $z^2$ , and putting  $r=0.9$  and  $\omega T=30^\circ$  gives  $y(n)=$

$$1.56 \cdot y(n-1) - 0.81 \cdot y(n-2) + x(n) - x(n-2)$$

The recurrence formula in this form can be used as the digital filter within a suitable program.

The general form of the recurrence formula for a second-order filter is

$$y(n) = b_0 \cdot x(n) + b_1 \cdot x(n-1) + b_2 \cdot x(n-2) + a_1 \cdot y(n-1) + a_2 \cdot y(n-2)$$

Its realization diagram is shown in Fig. 3, and in this example the coefficients are

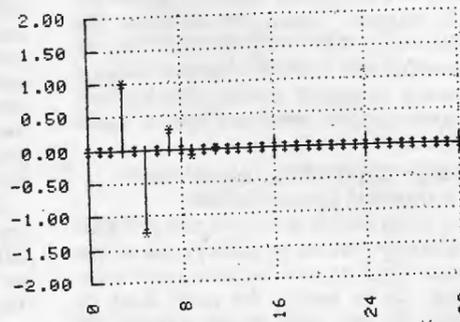
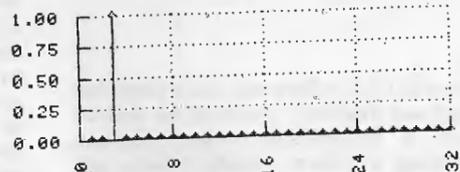
Output Values

- 0
- 0
- 0
- 1
- 1.25
- 0
- .3125
- 0
- .078125
- 0
- .0195313
- 4.08281E-03
- 0
- 1.2207E-03
- 0
- 3.05176E-04
- 0
- 7.62939E-05
- 0
- 1.90735E-05
- 0
- 4.76837E-06
- 0
- 1.19209E-06
- 0
- 2.98023E-07
- 0
- 7.46050E-08
- 0
- 1.86265E-08

INPUT

$$y(n) = b_0 \cdot x(n) + b_1 \cdot x(n-1) + b_2 \cdot x(n-2) + a_1 \cdot y(n-1) + a_2 \cdot y(n-2)$$

OUTPUT



**Fig. 8.** Oscillation caused by the impulse at the input soon dies away, as one would expect from a low-Q circuit.



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x coefficients      y coefficients

$$\begin{aligned} b_0 &= 1 & a_1 &= 1.56 \\ b_1 &= 0 & a_2 &= -0.81 \\ b_2 &= -1 & & \end{aligned}$$

The x-coefficients relate to the zero positions, while the y coefficients relate to the pole positions.

The output is of course a list of sample values, which has to be converted to an output signal with a d-to-a convertor and (usually) a low-pass filter. The values and

output signal in sampled data form are shown at Fig. 4 for a single unit input, and is the impulse response of the filter. As expected, the output oscillates at  $\frac{1}{2}$  of the sampling frequency and decays exponentially.

**Design filter with simple arithmetic suitable for a primitive microprocessor**

Sampling frequency, resonant frequency, and damping factor must be chosen so that they relate by simple ratios. In this case the pole positions are chosen so that they are at  $\frac{1}{2}$  the maximum frequency (i.e. at an angle of 90 degrees) and at a radius of  $\frac{1}{2}$ , Fig. 5. The poles are at  $+j0.5$  and  $-j0.5$ , the zeros are at  $+1$  and  $-1$ .

$$H(z) = \frac{z^2 - 1}{z^2 - 2r z \cos \omega T + r^2}$$

as before but  $r=0.5$  and  $\cos \omega T = \cos 90^\circ = 0$

$$\therefore H(z) = \frac{z^2 - 1}{z^2 + .25}$$

Alternatively this could be found by describing the transfer function in terms of the poles and zeros as follows:

$$H(z) = \frac{\text{position of zeros}}{\text{position of poles}} = \frac{(z+1)(z-1)}{(z+j0.5)(z-j0.5)}$$

and multiplying it out. The recurrence formula is obtained from the transfer function:

$$H(z) = \frac{Y(z)}{X(z)} = \frac{z^2 - 1}{z^2 + 0.25}$$

$$\therefore Y(z) \cdot z^2 + 0.25 Y(z) = X(z) \cdot z^2 - X(z)$$

$$\therefore y(n+2) + 0.25 y(n) = x(n+2) - x(n)$$

$$\therefore y(n) = x(n) - x(n-2) - 0.25 y(n-2)$$

Fig. 6 shows the realization diagram, Fig. 7 the spectrum and Fig. 8 the impulse response. The filter was designed with the very simple arithmetic of a primitive microprocessor in mind, limiting the processes to addition, subtraction and multiplication or division by two only. The result is a response curve which is too flat, Fig. 7. Of course a sharper response can be obtained with only a modest improvement in the arithmetic, as in the first example in which the coefficients are 1.56 and  $-0.81$ .

To be concluded with fourth-order Butterworth filter design.

# NEW PRODUCTS

## POWER ANALYSIS

Three displays are available on the 636 multifunction power analyser. The first two display voltage and current but the third shows a function selected from a push-button panel. The selected function may be watts, watthours, vars, varhours, volt-ams, power factor, phase angle and frequency.

The resolution of the instrument is 0.01% of full scale with an error of  $\pm 0.05\%$  of full scale. It will give true r.m.s. readings of sinusoidal or distorted waveforms at a frequency range of 40 to 400Hz.

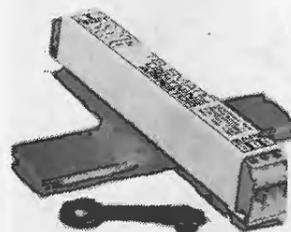
Voltage and current inputs are fully isolated with voltage ranges from 15 to 600V in six ranges with five significant figures; current is measured in nine ranges from 25mA to 55A.

A wide range of applications are possible with the instrument. They include calibration standards for meters and transducers; measurement of losses in transformers, inductors and motors; non-destructive testing of soft magnetic materials; power factor measurement in reactive loads; measuring phase; checking line-frequency stability; measuring the efficiency of lighting and heating circuits. Wessex Electronics Ltd, 114-116 North Street, Downend, Bristol BS16 5SE. **WW301**

## LIGHTNING ARRESTED

According to many sources, lightning strikes can generate up to 200A of surge current lasting for, typically 5µs, in an overhead line. The SA series of surge arrestors form Telematic are capable of withstanding 5kA peaks for over 10ms. While this is happening at the 'line' side of the arrestor, the 'safe' end remains at predetermined levels, safe for semiconductor circuitry. In the event of a surge greater than the design of the device, a 'fail-safe' mechanism will short circuit the input and isolate any series elements.

Thus modems, duplexers, two-wire transmitters, control loops, exchanges and all data transmission ports are fully protected. The arresters are approved for use with



British Telecom equipment. Physically small, 168mm long, the arrestor is bolted to an earthed busbar by a single bolt. Several arrestors can be mounted together and for outdoor use, weatherproof boxes are available. Telematic Ltd, 49 Hazelwood Drive, St Albans, Herts AL4 0UP. **WW302**

## TAPE NOISE REDUCTION

A tape compatibility unit, the TCU 3000a, is the first product of a new British company, Tardis Ltd. It claims to eliminate tape hiss entirely. The circuit is a two-to-one compander using an averaging system with treble pre- and de-emphasis. It is based around the Signetics NE570N dual compander chip, which can be switched to encode or decode.

High-frequency noise pumping, which is a problem with most compansion systems, is minimized by boosting the components of the signal above 2kHz by 12dB prior to encoding. Low-frequency pumping is reduced by a -12dB attenuation filter in series with the variable gain cell.

Tape saturation is avoided both by the two-to-one compansion system and by the introduction of a bandpass filter.

The performance figures claimed for the machine include a 40dB noise reduction, total harmonic distortion of 0.1% over the whole encode/decode cycle with a frequency response level between 30Hz and 30kHz. The dynamic range is claimed to be doubled.

The unit is connected between an amplifier and a tape recorder by phono plugs and it is not suitable for DIN level machines. It may only be used in one direction at a time - either record or replay - and so may not be used in a monitor mode for, say, a three-head recorder. The manufacturers have said that a two-way unit is to be made. Input from the amplifier is preset through a hole in the back of the case and once set does not need to be adjusted further.

In the other direction there is no input control for the level from the tape deck, so it is necessary to use a deck with an output level control. Input and output levels are indicated on two p.p.ms, one for each channel. After the input level is set the only controls used are three push buttons on the front panel: power switch, record or replay and unit switched in or out. This last control by-passes the unit so that the amplifier is connected directly to the tape deck.

Auditioning a pre-production unit, we found that the unit worked very well on music with no audible background noise at all. Some pumping was discernible on speech which was not evident as noise as much as a peculiar change in perspective between presence or absence of sound. The unit costs £149.50 inclusive and is available from the manufacturer, Tardis Ltd, Unit 3, Sunningdale Road, South Park Industrial Estate, Scunthorpe, South Humberside. **WW303**

## MULTI-WAVE GENERATOR

A number of user-defined waveforms may be stored in the memory of the waveform generator from 3D.

Function generators can normally supply square, sinusoidal, triangular or other regular waveforms but if any special function is required, it may take much adaptation of filters and shaping circuitry to get the required form. This generator interfaces with a microcomputer which can store up to 32 different waveforms. The frequency can be easily controlled up to 500kHz, with an output voltage of up to 10V r.m.s. and frequency sweeps, amplitude or frequency modulation are possible. A number of standard waveforms; sine, triangular, square, pulse etc. are already programmed into the generator's internal rom; others can be programmed and stored in eprom if they are to be used regularly. Applications cited by the manufacturer include component testing, vibration testing and the

testing of the reaction to stimulus of muscles and nerve tissue subject to the influence of various medicines. The generator is one of a series of Inlab modules and shares the same interface system which can be connected to a wide range of microcomputers through the IEEE-488 instrumentation bus, or may be configured to work with many others. Digital Design and Development, 18-19 Warren Street, London W1P 5DB **WW304**

## UV FOR P.C.B.s

An exposure unit for photosensitive coated copper boards or labels from Electronic Assistance includes four 15V actinic u.v. fluorescent tubes controlled by a precision timer. The UV-800 has an exposure area of 800cm<sup>2</sup> and boards are clamped against the exposure window by a flame-retardant foam pressure pad in



the lid. A microswitch prevents u.v. emission reaching the operator when the lid is raised. The exposure unit costs £85 (+ v.a.t.) and there is a smaller unit, UV-300, without the timer but with the same safety features, for £35 (+ v.a.t.). Electronic Assistance Ltd, Unit 1, Brunberth Industrial Estate, Rhayader, Powys LD6 5EN. **WW305**

## LCDs WORK IN THE COLD

Operating temperatures of -45° up to +85°C are claimed for the Survivor range of liquid crystal displays. At the lowest temperature there is a response time of 1.1s. The l.c.d.s are sealed with contact protection to allow the displays to work in 95% relative humidity and are also protected against shock and vibration to make them suitable for all sorts of hostile environments. Manufactured in Canada by Data Images Inc, they are available in the UK through Antech Electronics Ltd, Grenfell Place, Maidenhead, Berks SL6 1HL. **WW306**

# NEW PRODUCTS

## UNINTERRUPTABLE SWITCH-MODE POWER

Pmos high-speed switching transistors are used in a range of 125W power units, the SMM series from Elba Electric GmbH. Several models are available with up to five isolated outputs. One output may be used to charge a 24V battery, which can take over the power supply in the event of a mains failure.

Inputs may be 115 or 230V alternating or 24V direct. Outputs offered are 5V at 20A, 5 to 18V at 3A, -5 to -15V at 1A, 12 to 24V at 2.5A and 24 to 27.5V at 1A for battery charging. Outputs are short circuit protected. All this fits into a space 300 x 125 x 75mm. The units comply with standard safety regulations and are available in the UK through Dome Electronics, 1A Junction Road, Andover, Hants.

WW307

## FORTH COMPUTER ON A BOARD

Designed for system control applications, the TDS 900 is based on the Hitachi HD6301P 8/16-bit microprocessor and has an on-board Forth interpreter. Fitting on a standard Eurocard, the TDS900 is provided with 10K of ram and 8K of rom. Either or both of these can be easily extended by the addition of TDS940 extension cards to give 160K-bytes of ram or 640K-bytes of rom. An RS232C connector is incorporated and can be connected to a v.d.u. and to an eprom programmer.

The computer is intended chiefly for installing into equipment and a typical development cycle is to programme the computer using a v.d.u. with the full-screen editor

included in the on-board software. The program is entered in Forth, which is then compiled into the Forth dictionary format. The program may be run and tested (debugging is inherent in the Forth language) and then output to a prom programmer. The eprom may then be plugged in to the computer which thus becomes dedicated to that task. Even when it is installed in the equipment, the computer can be connected to a v.d.u. and its operation may be monitored and corrected if necessary.

A large variety of input/output interfaces may be connected to the computer including a-to-d or d-to-a converters, control signals to triacs or other switches, printers, keyboards, or displays.

Standard Fig-Forth language is used with additional commands for the screen editor and for some functions, for example timing. Any function not included can, of course, be added by the user.

One application developed by the manufacturer was a sound-operated switch which could be used by the severely handicapped to operate up to ten appliances such as switching on or off lighting, the tv, radio, etc. or for summoning assistance.

The computer is produced in different versions: cmos for battery-powered operation or the cheaper n-channel version; there are also lower cost versions with less ram. The full memory cmos model costs £179.95 for one-off, less for quantity orders. Triangle Digital Services Ltd, 23 Campus Road, London E17 8PG.

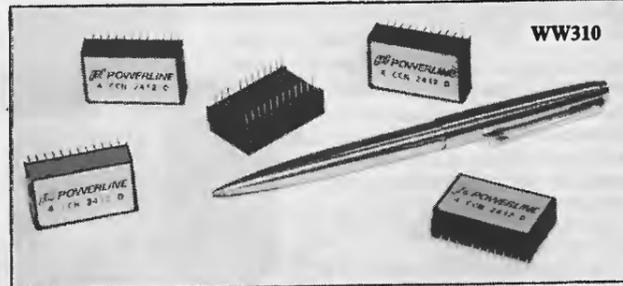
WW308

## FLAT CABLE TERMINALS

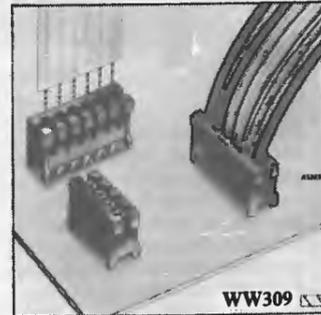
Connectors which are soldered to a p.c.b. can have the flat cable inserted with no force. The housing is then pushed down to effect the connection. No special tools or cable preparation are necessary with the Snap-mate connectors and the cables may be easily released by lifting the housing. Connectors are available for 2, 3, 4, 5 and 6-conductor cables. The gas-tight high-pressure contact principle used in the terminals is claimed to offer as reliable connections as in gold-plated contacts while using the lower cost tin alloy plating. Burndy Ltd, Connector House, Colney Street, St Albans, Herts AL2 2ED.

WW309

If you would like more information on any of the items featured here, enter the appropriate WW reference number(s) on the mauve reply-paid card.



WW310



WW309

## D.C. TO D.C.

The first of a series of d.c.-to-d.c. converters are thick-film hybrids in 24-pin d.i.ps with up to 4W of output power in both regulated and unregulated versions. Output voltages of 5, 12, 15, -12 and -15V are derived from models with input voltages nominally of 5, 12, 24, 28 and 48V. The makers claim that the use of thick film techniques increases

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the reliability and provides twice as much output power as discrete component versions of a similar size. Powerline Electronics Ltd, 5 Nimrod Way, Reading, Berks RG2 0EB.

## EDUCATIONAL KIT

Thirty-one different experiments and applications are possible with the experimental electronics kit from Cambion. Two years of planning have gone into the development of the kit which comes complete with teacher's notes and a series of worksheets. The electronic components plug into a breadboard and may be re-used in different configurations.

Designed for use in schools, the kit is equally useful in industrial schemes for training apprentices. It costs just under £30 from Cambion Electronics Products Division, Midland Ross Corporation, Cambion Works, Castleton, Sheffield S30 2WR.

WW311

# U.K. RETURN OF POST MAIL ORDER SERVICE, ALSO WORLDWIDE EXPORT SERVICE

## RECORD DECKS SINGLE PLAY 11in Turntables 240 volt AC. Post £2

Make	Model	Drive	Cartridge	Price
BSR	P204	Rim	Magnetic	£20
BSR	P170	Rim	Ceramic	£20
BSR	P232	Belt	Ceramic	£24
GARRARD	6200	Rim	Ceramic	£22
GARRARD	Delux	Belt	Magnetic	£40

BSR	P204	9 volt	Ceramic	£18
BSR	P232	12 volt <td>Magnetic</td> <td>£24</td>	Magnetic	£24

## AUTOCHANGERS 240 VOLT

BSR	Budget	Rim	Ceramic	£16
BSR	Delux	Rim <td>Ceramic</td> <td>£18</td>	Ceramic	£18

## HEAVY METAL PLINTHS

Cut out for most BSR or Garrard decks. Silver grey finish, black trim. Size 16 x 13 3/4 in. **£4**

## DECCA TEAK VENEERED PLINTH. Post £1.50

Superior finish with space and panel for small amplifier. Board is cut for B.S.R. 18 3/4 in. x 14 1/4 in. x 4 in. Black/chrome fascia trim. Also with boards cut out for Garrard £3. Tinted plastic cover £5 **£5**

## TINTED PLASTIC COVERS

17 7/8 x 13 1/2 x 3/4 in.	£3	18 1/4 x 12 1/2 x 3 in.	£5
17 1/4 x 9 3/8 x 3/4 in.	£3	14 3/8 x 12 1/2 x 2 7/8 in.	£5
16 1/2 x 15 x 4 1/2 in.	£5	16 3/8 x 13 x 4 in.	£5
17 x 12 1/2 x 3 1/2 in.	£5	14 1/2 x 13 1/2 x 2 3/4 in.	£5
22 3/8 x 13 7/8 x 3 in.	£5	17 1/4 x 13 3/4 x 4 1/8 in.	£5
21 1/2 x 14 1/2 x 2 1/2 in.	£5	21 x 13 7/8 x 4 1/8 in.	£5
23 3/4 x 14 x 3 1/8 in.	£5	30 3/4 x 13 3/8 x 3 1/4 in.	£5

## THE "INSTANT" BULK TAPE ERASER

Suitable for cassettes and all sizes of tape reels. AC mains 200/250V. Hand held size with switch and lead (120 volt to order). Will also demagnetise small tools and computer tapes. **Head Demagnetiser only £5.**

## BATTERY ELIMINATOR MAINS TO 9 VOLT D.C.

Stabilised output, 9 volt 400 ma. U.K. made in plastic case with screw terminals. Safety overload cut out. Size 5 x 3 1/4 x 2 1/2 in. Transformer Rectifier Unit. Suitable Radios, Cassettes, models, £4.50. Post 50p.

## DE LUXE SWITCHED MODEL STABILISED. £7.50. PP £1.

3-6-7-9 volt 400ma DC max. Universal output plug and lead. Pilot light, mains switch, polarity switch.

## DRILL SPEED CONTROLLER/LIGHT DIMMER KIT. Easy build kit. Controls up to 480 watts AC mains. £3. PP 65p.

DE LUXE MODEL READY-BUILT 800 watts. Front plate fits standard box. £5. Post 65p.

## EMI 13 1/2 x 8 in. LOUSPEAKERS

Model 450A, 10 watts R.M.S. with moving coil tweeter and 16W 2-way crossover; 3 ohm or 8 ohm. "Final Clearshield" £8 **£8**

## SUITABLE BOOKSHELF CABINET

Teak Veneers £6.50. Size 18 x 11 x 6 in. Post £1.50.

## RELAYS. 6V DC 95p. 12V DC £1.25. 18V £1.25. 24V £1.30

ALUMINIUM CHASSIS. 6 x 4 - £1.75; 8 x 6 - £2.20; 10 x 7 - £2.75; 12 x 8 - £3.20; 14 x 9 - £3.60; 16 x 6 - £2.50; 16 x 10 - £3.80; 12 x 3 £2.20; 14 x 3 £2.50.

## ALUMINIUM PANELS. 6 x 4 - 55p; 8 x 6 - 90p; 14 x 3 - 90p; 10 x 7 - £1.15; 12 x 8 - £1.30; 12 x 5 - 90p; 16 x 6 - £1.30; 14 x 9 - £1.75; 12 x 12 - £1.80; 16 x 10 - £2.10.

## ALUMINIUM BOXES. 4 x 4 x 1 1/2 £1.20. 4 x 2 1/2 x 2 £1.20. 3 x 2 x 1 £1.20. 6 x 4 x 2 £1.90. 7 x 5 x 3 £2.90. 8 x 6 x 3 £3. 10 x 7 x 2 1/2 £3.60. 12 x 5 x 3 £3.60. 12 x 8 x 3 £4.30.

## ALI ANGLE BRACKET 6 x 3/4 x 3/4 in. 30p.

## BRIDGE RECTIFIER 200V PIV 2a £1. 4a £1.50. 6a £2.50.

## TOGGLE SWITCHES SP 40p. DPST 50p. DPDT 60p.

## MINIATURE TOGGLES SP 40p. DPDT 60p.

## RESISTORS. 100 to 10M. 1/4W, 1/2W, 1W, 2p; 2W 10p.

## LOW ohm 1 watt 0.47 to 3.9 ohms 10p.

## HIGH STABILITY. 1/2w 250 10 ohms to 1 meg. 10p.

## WIRE-WOUND RESISTORS 5 watt, 10 watt, 15 watt 20p.

## PICK-UP CARTRIDGES SONOTONE 9TAHC £2.80.

## BSR Stereo Ceramic SCT Medium Output £2. SC12 £3.

## PHILIPS PLUG-IN HEAD. Stereo Ceramic. AU1020 (G306 - GP310 - GP233 - AG3306. £2. A.D.C., OLM 30/3 Magnetic £5.

## GOLDRING G850 £6.50, G800 £8.50. STYLUS most Ceramic Acos, Sonotone, BSR, Garrard Philips Diamond £1.20 ea.

## MAGNETIC STYLUS, Sony, JVC, Sanyo, Goldring, etc. £4.

## LOCKTITE SEALING KIT DECCA 118. Complete £1.

## VALVE OUTPUT Transformers 15 watt £14; 30W £18; 50W £20; 100W £24. Post £2.

## SUB-MIN MICROSWITCH, 50p. Single pole changeover.

## ANTEX SOLDERING IRON "C" 15W £4.60. 25W "X25" £4.70.

## WAFER SWITCHES. 1 1/4" dia. 60p ea.

## 1P 12W; 2P 2W; 2P 6W; 3P 4W; 4P 2W; 4P 3W.

## FERRITE ROD. 6" x 1/2"; 6" x 3/8"; 8 x 5/16" 40p.

## XLR Lead Plug £2.40. Lead socket £2.75.

## XLR Chassis Plug £2.20. Chassis Socket £2.55.

## BANANA 4mm Plugs/Sockets, red/black 20p.

## JACK PLUGS Mono Plastic 25p; Metal 30p. Sockets 25p.

## JACK PLUGS Stereo Plastic 30p; Metal 35p. Sockets 30p.

## FREE SOCKETS - Cable end 30p. Metal 45p.

## 2.5mm and 3.5mm JACK SOCKETS 25p. Plugs 25p.

## DIN TYPE CONNECTORS

## Sockets 3-pin, 5-pin 15p. Free Sockets 3-pin, 5-pin 25p.

## Plugs 3-pin 20p; 5-pin 25p; Speaker plugs 25p; Sockets 15p.

## PHONO PLUGS and SOCKETS ea. 20p; Double sockets 30p.

## Free Socket for cable end 20p. Screened Phono Plugs 25p.

## B.N.C. PLUGS £1. Sockets £1. Free Sockets £1.10.

## U.H.F. PLUGS 50p. Sockets 50p. Reducers 20p. Couplers 50p.

## 300 ohm TWIN RIBBON FEEDER 10p yd.

## 300 ohm to 75 ohm AERIAL MATCHING TRANSFORMER £1.

## U.H.F. COAXIAL CABLE SUPER LOW LOSS, 75 ohm 25p yd.

## COAX PLUGS 30p. COAX SOCKETS 30p. Lead Sockets 65p.

## NEON INDICATORS 250V, round 40p. Rectangular 45p.

## POTENTIOMETERS Carbon Track

5kΩ to 2MΩ. LOG or LIN. L/S 50p. DP 90p. Stereo L/S £1.10. DP £1.30. Edge Pot 5K. SP 45p.

### MINI-MULTI TESTER NEW

De luxe pocket size precision moving coil instrument. Impedance + Capacity - 4000 o.p.v. Battery included. 11 instant ranges measure: DC volts 5.25, 250, 500. AC volts 10, 50, 500, 1000. DC amps 0-250µA, 0-250mA. Resistance 0 to 600k ohms. **£6.50** Post 50p

De Luxe Range Doubler Model, 50,000 o.p.v. £18.50. 7 x 5 x 2 in. Post £1. 43 Ranges, 1,000V, AC-DC, 20 meg, etc.

### PANEL METERS

50µA, 100µA, 500µA, 1ma, 5ma, 50ma, 100ma, 500ma, 1 amp, 2 amp, 25 volt, VU 2 1/4 x 2 x 1 1/4. Stereo VU 3 1/4 x 1 1/4 x 1 in. **£4.50** Post 50p

### RCS SOUND TO LIGHT CONTROL BOX

Complete ready to use with cabinet size 9 x 3 x 5 in. 3 channel, 1000 watt each. For home or disco input 200mV to 100 watt. AC 200/250V. Post £1. OR KIT OF PARTS £19.50. LESS CABINET £15. Disco bulbs 100 watt, blue, green, yellow, red, amber, screw or bayonet £2 each. Post £1.50 per six. Rope lights, 4 channel, 11ft with controller £33. PP £1. "FUZZ" lights, red, blue, green, amber, 240V. £23. Post £1. 200 Watt Rear Reflecting White Light Bulbs. Ideal for Disco Lights, Edison Screw. 6 for £4, or 12 for £7.50. Post £1.50. Suitable panel mounting holders 85p.

### RCS "MINOR" 10 watt AMPLIFIER KIT £14

This kit is suitable for record players, guitars, tape playback, electronic instruments or small PA systems. Two versions available: Mono, £14; Stereo, £20. Specification 10W per channel; size 9 1/2 x 3 x 2 in. SAE details. Full instructions supplied. 240V AC mains. Post £1.

### RCS STEREO PRE-AMP KIT. All parts to build this pre-amp. Inputs for high, medium or low imp per channel, with volume control and PC Board. Can be ganged to make multi-way stereo mixers **£3.50** Post 65p

### MAINS TRANSFORMERS

250-0-250V 80mA, 6.3V 3.5A, 6.3V 1A **£8.00** £2  
350-0-350V 250mA, 6.3V 6A CT **£12.00** £2  
220V 25ma 6V lamp £2.50. 220V 45ma 6V 2 Amp **£4.00** £1  
250V 60mA, 6V 2A **£4.75** £1

## AUTO

## GENERAL PURPOSE LOW VOLTAGE

Tapped outputs available	Price Post
2 amp, 3, 4, 5, 6, 8, 9, 10, 12, 15, 18, 25 and 30V	£8.00 £2
1 amp, 6, 8, 10, 12, 16, 18, 20, 24, 30, 36, 40, 48, 60	£8.00 £2
2 amp, 6, 8, 10, 12, 16, 18, 20, 24, 30, 36, 40, 48, 60	£10.00 £2
3 amp, 6, 8, 10, 12, 16, 18, 20, 24, 30, 36, 40, 48, 60	£12.50 £2
5 amp, 6, 8, 10, 12, 16, 18, 20, 24, 30, 36, 40, 48, 60	£18.00 £2
5-8-10-16V 1/2 amp. £2.50 £1	15-0-15V 1 amp. £4.00 £1
6V 1/2 amp. £2.00 £1	15-0-15V 2 amps. £4.50 £1
6-0-6V 1 1/2 amp. £3.50 £1	20-0-20V 1 amp. £4.00 £1
9V 250ma. £1.50 £1	20-0-20V 2 amp. £4.50 £1
9V 3 amp. £4.50 £1	20-0-60V 1 amp. £4.50 £2
8-0-8V 50ma. £1.50 £1	25-0-25V 2 amps. £5.50 £1
9-0-9V 1 amp. £2.50 £1	28V 1 amp Twice. £6.00 £2
10-0-10V 2 amps. £4.00 £1	30V 1/2 amp. £4.50 £1
10-30-40V 2 amps. £4.50 £1	30V 5 amp and. £5.50 £2
12V 100ma. £1.50 £1	17-0-17 2a. £5.50 £2
12V 300ma. £2.50 £1	35V 2 amps. £4.50 £1
12V 3 amps. £4.50 £1	17-0-17 30-0-30V 4a. £10.00 £2
12-0-12V 2 amps. £4.50 £1	and 20-0-20V 2a. £10.00 £2

## CHARGER TRANS

Post RECTIFIERS

6-12 volt 3a	£4.50+£2	6-12 volt 2a	£1.10+80p
6-12 volt 4a	£5.50+£2	12 volt 2a	£2.00+80p

## 'OPUS COMPACT SPEAKERS £22 pair' Post £2

TEAK VENEERED CABINET 11 x 8 1/2 x 7 in, 15 watts 10 to 14,000 cps. 4 ohm or 8 ohm

## OPUS TWO 15 x 10 1/2 x 7 3/4 in 25 watt 2-way system £39 pair. Post £3

## LOW VOLTAGE ELECTROLYTICS Wire ends

10p  
1mf, 2mf, 4mf, 8mf, 10mf, 16mf, 25mf, 30mf, 50mf, 100mf, 250mf. All 15 volts. 22 mf/6V/10v; 25 mf/6V/10v; 47 mf/10V; 50 mf/6V; 68 mf/6V/10V/16V/25V; 100 mf/10V; 150 mf/6V/10V; 200 mf/10V/16V; 220mf/4V/10V/16V; 330 mf/4V/10V; 500mf/6V; 680 mf/10V; 1000mf/10V/16V/25V/4V/10V; 1500mf/12V; 2200mf/6V/10V; 3300mf/6V; 4700mf/4V/10V; 500mF 12V 15p; 25V 20p; 50V 30p; 100mF 100V £1.20.

## NON POLARISED CAPACITORS - REVERSIBLE

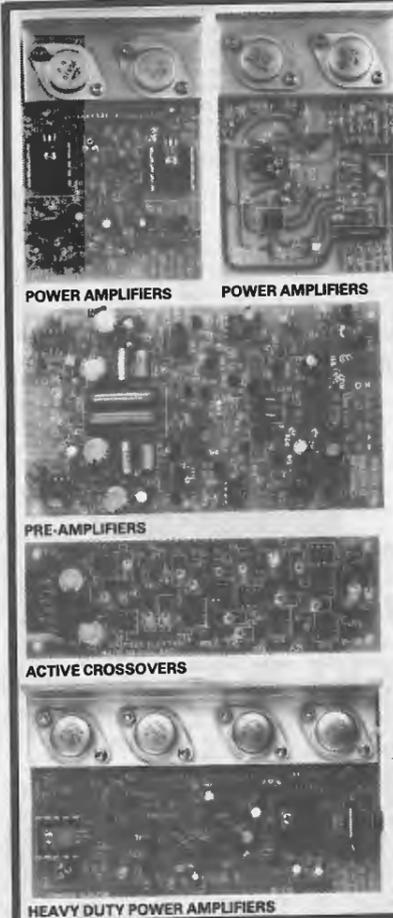
1mF 250V 25p; 1.5mF 100V 25p; 2.2mF 250V 30p; 3.3mF 100V 40p; 4.7mF 100V 40p; 10mF 63V 40p; 32mF 50V 25p.

## HIGH VOLTAGE ELECTROLYTICS

2/500V 45p 32+32+16/350V 90p 8+16/450V 75p  
8/450V 45p 100+100/275V 85p 16+16/350V 80p  
16/350V 45p 150+200/275V 70p 32+32/350V 85p  
32/500V 95p 32+32+32/325V 75p 32+32/500V £1.80  
32/350V 50p 50+50+50/350V 95p 50+50/300V 50p  
50/450V 95p 8+8/500V £1 80+40/500V £2

## CAPACITORS WIRE END High Voltage

.001, .002, .003, .005, .01, .02, .03, .05 mfd 400V 5p.  
.1Mf 200V 5p. 400V 10p. 600V 15p. 1000V 25p.  
.22Mf 350V 12p. 600V 20p. 1000V 30p. 1750V 50p.  
.47M



# WHAT ARE YOU DRIVING?

**INDUCTION LOOP TRANSMITTERS  
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**CRIMSON ELEKTRIK POWER AMP MODULES HAVE DONE IT ALL**

CHOOSE our acclaimed Bipolar Modules for the best in Hi-Fi. These modules have been widely used by professional bodies. They are high slew, low t.h.d. devices without need for the output fuses that spoil fidelity. They have instantly resettable 'electronic fuse' and are L-bracket mounting for flexi installation.  
CHOOSE Our Mosfet Modules for the most difficult loads. These modules are rugged and make ideal line step-up transformer drivers. They respond down to d.c. and make excellent servo-driving devices. They have low d.c. offset drift due to jfet inputs.

BIPOLAR	TYPE	MAX. O/P POWER	SUPPLY TYP.	VOLTAGE MAX.	THD TYP.	PRICE INC.
						V.A.T. & POST
	CE 808	60W/8Ω	± 35	± 40	< .01%	£21.50
	CE 1004	100W/4Ω	± 35	± 40	< .018%	£25.00
	CE 1008	120W/8Ω	± 45	± 50	< .01%	£28.00
	CE 1704	200W/4Ω	± 45	± 63	< .015%	£35.50
	CE 1708	180W/8Ω	± 60	± 63	< .01%	£35.50
	CE 3004	320W/4Ω	± 60	± 63	< .02%	£49.50
MOS	FE 908	90W/8Ω	± 45	± 60	< .01%	£30.00
	FE 1704	170W/4Ω	± 45	± 60	< .025%	£39.00

Export - no problem. Please write for quotation or quote your Master Charge card number.

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PHOENIX WORKS, 500 KING STREET, LONGTON  
STOKE-ON-TRENT, STAFFS  
TEL: 0782 330520

Pye Europa MF5FM high-band sets, complete but less mike and cradle. £90 each plus £2 p.p. plus VAT.  
Pye M294 high-band FM sets, complete but less mike, speaker and cradle. £150 each plus £2 p.p. plus VAT.  
Pye Reporter MF6 AM high-band sets, complete but less speaker and cradle. £90 each plus £2 p.p. plus VAT.  
Pye Olympic M201 AM high-band sets, complete but less mike, speaker and cradle. £90 each plus £2 p.p. plus VAT.  
Pye Westminster W15 FM G band 42-54 MHz sets, unused and like new, but less mike, speaker and cradle. £65 each plus £2 p.p. plus VAT.  
Pye Westminster W15 AMD mid-band multi-channel sets, no mikes, speakers or cradles. £45 each plus £2 p.p. plus VAT.  
Pye Westminster W15 AMD mid-band crystallized and converted to 129.9 MHz, 130.1 MHz, 130.4 MHz. Very good condition. £120 each plus £2 p.p. plus VAT.  
Pye Westminster W15 AMD high-band and low-band sets available. Sets complete but less mikes, speakers and cradles. £70 each plus £2 p.p. plus VAT.  
Pye Westminster W30 AM low-band sets only, no control gear. Sets complete and in good condition. £45 each plus £2 p.p. plus VAT.  
Pye base station F30 AM, low band and high band available, remote and local control. Prices from £220 plus VAT.  
Pye base station F401 high-band AM, local control, fully solid state, complete but less mike. £275 each plus £15 p.p. plus VAT.  
Pye base station receiver R402 high-band FM 148-174MHz, single channel, 12.5 KHz channel spacing. £95 each plus £5 p.p. plus VAT.  
Pye base station F9U, remotely controlled, 5 Watt output, UHF (440-470 MHz), single channel. £90 each plus £5 p.p. plus VAT.  
Pye base station F412 UHF (440-470 MHz), 25KHz channel spacing, single channel, local control. £250 each plus £15 p.p. plus VAT.  
Pye Beaver M254 high-band FM sets, 15 Watt, robust mobile radiotelephones for industrial use, sets complete but less crystals, as new condition. £120 each plus £2 p.p. plus V.A.T.  
Pye base station receiver F27 AM, crystallized on 116.46 MHz, can be recrystallized on air band. Unused condition. £15 each plus £5 p.p. plus VAT.  
Pye AC200 mains power unit for Olympic or Reporter, automatic standby power facility with trickle charging and built-in quartz digital clock. £95 each plus £5 p.p. plus VAT.

Pye AC power supply unit AC25PU, specially designed for use with the Europa series mobiles, power output 13.2 volt 5 amp. New condition. £45 each plus £5 p.p. plus VAT.  
Pye PC1 radiotelephone controller, good condition, two only at £50 each plus £2 p.p. plus VAT.  
Pye Tulip microphone as used on most base stations and PC1, 2400 ohm with pt switch. £15 plus £1 p.p. plus VAT.  
Pye PF1 UHF FM Pocketfone receivers, 440-470 MHz, single channel, int. speaker and aerial. Supplied complete with rechargeable battery and service manual. £6 each plus £1 p.p. plus VAT.  
Ni-Cad Batteries for Pye PF1, used but good condition, Rx (Yellow) £2 each Tx (Red). £3 each plus £1 p.p. plus VAT.  
Pye Pocketfone PF1 Battery Chargers, type BC14, 12 way with meter. £10 each plus £1 p.p. plus VAT.  
Pye Pocketfone PF1 Battery Chargers, type BC5 single charger, brand new. £20 each plus £1 p.p. plus VAT.  
Pye single sideband HF Mobile Radiotelephone, type SSB130M, 100 W P.E.P. output, 6-channel, 2-15 MHz. Complete and new condition but less power unit. £250 plus £10 p.p. plus VAT.  
Pye fixed station transmitter, type T100 FM, 'G' band 38.6-50 MHz, 100 W output. 25 KHz channel spacing. New condition. £100 each plus £10 p.p. plus VAT.  
Tektronix Oscilloscope Type 6A7A, solid state, 100 MHz bandwidth. £250 plus VAT.  
Hartley Oscilloscope Type CT436, valved, DC to 6 MHz bandwidth. £50 plus VAT.  
Uniradio 95 Co-axial cable 50 ohm miniature cable dia. 2.3 mm. £2 per 90 M plus VAT.  
Philips Telephone Power Units Type PE2004/02 48 volt 4 amps (new). £20 plus VAT.  
Agfa Videochrom Chromdioxid video cassette tape for use with Philips N1500/1700 VCR. LVC 120. £6 each plus £1 p.p. plus VAT.

**MAINS TRANSFORMERS**  
Mains isolating transformer, 500VA 240V input, 240V C.T. output, housed in metal box. £15 each plus £6 p.p. plus VAT.  
Mains isolating transformer, 240V tapped input, 240V 3 amp plus 12V 0.5 amp output. £20 each plus £6 p.p. plus VAT.  
Advance Volstat transformers, type CVN200/5, input 24 or 28V DC via inverter, output 220 or 240V RMS 150 watt, 50Hz. £10 each plus £4 p.p. plus VAT.

Marconi AM/FM signal generator, type TF995A/3/S (CT402), 1.5-220 MHz, good condition with copy of service manual. £95 each plus £15 p.p. plus VAT.  
Airmec millivolt meter, Type 301. £50 plus £2 p.p. plus VAT.  
Advance signal generator Type C2. £25 plus £5 p.p. plus VAT.  
Airmec modulation meter, Type 210. £75 plus £5 p.p. plus VAT.  
Marconi HF Spectrum analyser, Type OA1094A/S 0-30 MHz. £100 plus VAT (buyer collects).  
Eddystone receiver, Type 770U 144-500 MHz. £155 plus £5 p.p. plus VAT.  
Servomex AC voltage stabiliser, type AC2, 240V @ 9 amp. £45 each plus £15 p.p. plus VAT.  
Servomex AC voltage stabiliser, type AC7, 240V @ 20 amp. £75 each plus £15 p.p. plus VAT.  
Samwell & Hutton T.V. Wobulator, type 78M, 16-230 MHz. £35 each plus £15 p.p. plus VAT.  
Rhode & Schwarz power signal generator 0.1 to 30 MHz, Type BN41001. £50 plus £10 p.p. plus VAT.  
Rhode & Schwarz wide band signal generator 10 Hz to 10 MHz, Type BN40861. £50 plus VAT.  
Rhode & Schwarz sweep signal generator, 50 KHz to 12 MHz, Type BN4242/2. £50 plus VAT.  
Meguro signal generator, type MSG-230E, 16 KHz-50 MHz. £130 plus £10 p.p. plus VAT.  
Rhode & Schwarz Polyskop Type SWOB BN4244, 0.5 MHz to 400 MHz. £150 plus £15 p.p. plus VAT.  
Computer-grade electrolytic capacitors, screw terminals, 25,000mfd., 33 volts, brand new. £1 each plus 50p p.p. plus VAT.  
60 amp alternator and general noise filters for use in vehicles. £1 each plus 50p p.p. plus VAT.  
Modern telephones, type 746, with dials, colour grey, used but good condition. £8 plus £1 p.p. plus VAT.  
Cigar lighter plug with lead. £1 each plus 30p p.p. plus VAT.  
IC test clips, 28-way and 40-way, gold plated. £2 each plus 30p p.p. plus VAT.  
Equipment wire, size 7/0.2mm, colour yellow, 500-metre reels. £4 plus £1 p.p. plus VAT.  
Scotch video tape, 1" x 10" (25.40mm x 910mm), brand new. £5 each plus £2 p.p. plus VAT.  
Power units, 70 volt @ 8 amp, 20 volt @ 3 amp. Brand new but no details. £20 each plus £8 p.p. plus VAT.  
Beryllium block mounts for CCS1 valves, etc. £10 each plus £1 p.p. plus VAT.

## B. BAMBER ELECTRONICS

GOVERNMENT AND MANUFACTURERS' SURPLUS

5 STATION ROAD  
LITTLEPORT CAMBS CB6 1QE  
Telephone: Ely (0353) 860185

ELECTRONIC COMPONENTS  
TELECOMMUNICATION EQUIPMENT  
TEST GEAR



WW - 065 FOR FURTHER DETAILS

## TEST EQUIPMENT

Tek CA Plug-ins	£25
Tek M Plug-in	£80
Tek Z Plug-in	£80
Tek 7313 100MHz Storage Main Frame	£1800
Tek 7870 Plug-in	£295
H.P. 6920B Meter Calibrators	£25
H.P. 1400 series Plug-ins, from	£195
Texscan X-Y Display 12" DU120	£185
Telonic 121 X-Y Display 12"	£195
Wavetek 1601C X-Y Display 12"	£75
Fuke 8000A 3 1/2 digit DMM	£145
Fuke 8600A 4 1/2 digit DMM	£145
E.H. 132L Pulse Generator	£16
Avo Multimeter Model 5	£80
Avo Model Mk 5 - as new	£70
Avo Model 8X Panclimatic	£65
Avo Model 7	£65
Avo Model 8 Mk. III	£15
Leather Cases for Avo's	£15
Ever Ready Avo Case	£55
Rotronics 150KHz Sine/Sq. Sig. Gen.	£395
Tequipment DM64 Storage Scope	£395
Houston Digital Increment Plotter DP10	£175
Systron Donner 825A 8 digit 50MHz Timer/Counter	£50
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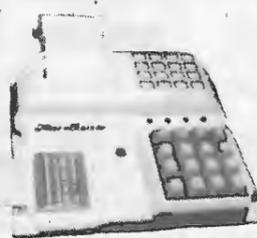
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# A COMPETITION OPEN TO ALL WIRELESS WORLD READERS WITH £8000 IN CASH PRIZES

Design an Electronic Device  
to help the Disabled

Could you design a piece of equipment to help a disabled person? If so, you would — in addition to undertaking this worthy task — be eligible to win a substantial cash prize.

Our competition is open to individuals or groups resident in the UK. You register your entry using the form below, sending it to the Editor to arrive at his office not later than June 30th 1983. The designs themselves must be submitted to his office by 1st October 1983.

Entries, which will be judged by a group of eminent engineers and doctors, must consist of the following: - a statement of the design objectives; an overall description of the device; detailed circuit descriptions and diagrams; a model of the device or a model of a unique aspect of the design sufficient to demonstrate its feasibility.

The finalists will be invited to London to talk over their entries with the judges and be awarded their prizes. The prizes are:

**1st prize £2,500**  
**2nd prize £1,500**

and the 4 runners up will be awarded prizes each of **£1,000**

To make sure you have the maximum time to undertake your design, return your entry form now!

## "DESIGN AN ELECTRONIC DEVICE TO HELP THE DISABLED" LIST OF RULES

- The competition is open to U.K. residents only.
- Entrants can be individuals or groups.
- All participants must register their interest in entering the competition on the form provided which must be returned to the Wireless World Editorial Department by the 30th June 1983.
- All entrants agree to give Wireless World first serial publication rights to an article describing the entry.
- All entrants indemnify Wireless World from any liability in respect of injury to people or damage to property arising from the use of the design.
- All submitted designs must be the original work of the entrant or entrants and must not infringe the rights of third parties in anyway.
- All submissions should consist of:
  - A statement of design objectives
  - An overall description of the device
  - Detailed circuit descriptions and diagrams
  - A model of the device or the unique aspect of the design sufficient to demonstrate its feasibility.
- The design will be judged on:
  - Originality and benefit to the handicapped
  - Potential for production
  - Elegance of engineering design
  - Electronics content
  - Design reliability
  - Simplicity of operation
  - Freedom from excessive maintenance
- A safety.
- Software only solutions are not accepted.

- The judges' decision is final.
- All designs must be submitted to the Wireless World Editor by the 1st October 1983.
- Shortlisted entrants must be prepared to travel to a venue in London sometime during November and December 1983 to demonstrate their design. All costs will be paid by the journal.
- Employers of Business Press International are not allowed to enter this competition.

## wireless world ENTRY FORM

"Design an electronic device to help the disabled"

Name of competitor \_\_\_\_\_

Address \_\_\_\_\_

Telephone (home) \_\_\_\_\_

(business) \_\_\_\_\_

I intend to enter the competition and to abide by the rules as laid down in the May 1983 issue of Wireless World.

I understand that, in order to qualify, my entry must be in the hands of the judges by 1st October, 1983

Signature \_\_\_\_\_

Date \_\_\_\_\_

Please send this form, as soon as possible, to:

The Editor, WIRELESS WORLD  
Room L302, Quadrant House, The Quadrant  
Sutton, Surrey SM2 5AS.

Receipt of the form will be acknowledged.

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AA174 0.15	ASZ63 2.50	BC222 0.11	BD179 2.00	BF302 0.34	GM4078AS 1.75
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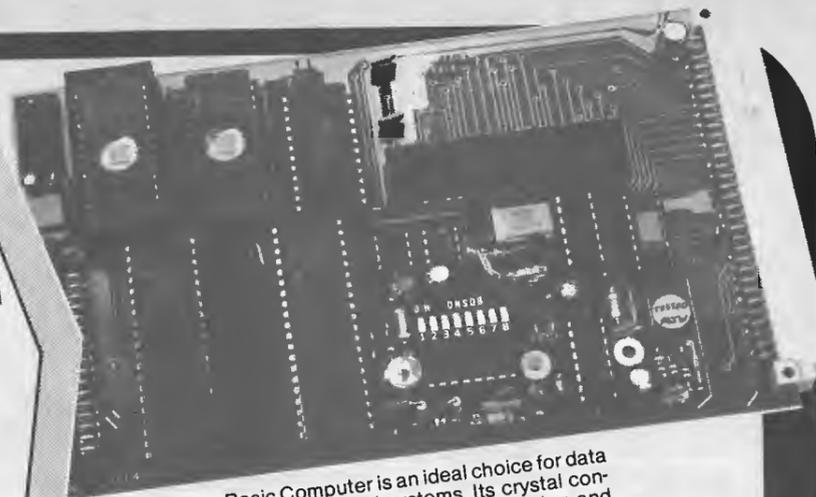
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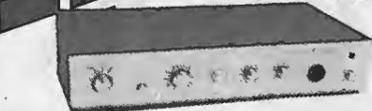


PUTTING THE BEST WITHIN YOUR GRASP

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# HART

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300 SERIES AMPLIFIERS



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Tuner, Complete Kit ..... £163  
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We have done two kits to this design, one using the original car cassette mechanism and the newer version using a very high quality front loading deck. This new deck has an excellent W & F performance and fitted with our latest Sendust Alloy Super Head gives an incredible frequency range (with good tape you can see 23KHz on ours!).

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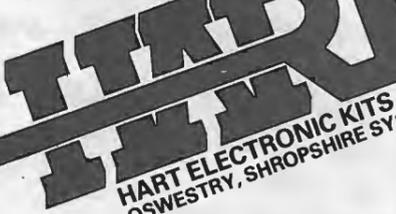
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# ELECTRIC SHOCK

## 2 WAYS TO RECOVERY

ACT AT ONCE - DELAY IS FATAL

### ELECTRIC SHOCK ACT AT ONCE - DELAY IS FATAL

**make sure it is safe to approach**  
If the casualty is not clear of the source of the shock break the current by switching off the circuit remaining the plug or pulling the cable free. If this is not possible stand on dry insulating material (rubber wood brick blocks) and use a long object to push or pull the casualty clear of the source using insulating material (such as bamboo) if available. Do not touch him with bare hands.

**if the casualty is breathing**  
Place casualty in the recovery position and roll medical aid.

**if the casualty is NOT breathing**  
start artificial respiration - speed is essential

**if AFTER FOUR INFLATIONS casualty does not respond to artificial respiration**  
external heart compression

1

Display the ELECTRICAL REVIEW shock first aid chart (356x508mm) supplied in thousands to destinations world-wide. Recent deliveries include consignments to companies in Papua New Guinea, Dubai, United Arab Emirates, The Philippines, apart from UK commercial and industrial, educational, Central Government, Local Authorities' orders.

2

Carry the ELECTRICAL REVIEW pocket-size shock card (92x126mm) designed to help safety and training officers, medical and welfare personnel; all who might find themselves called to save a life. Always pocket your card; there's a useful two-year calendar on the back.

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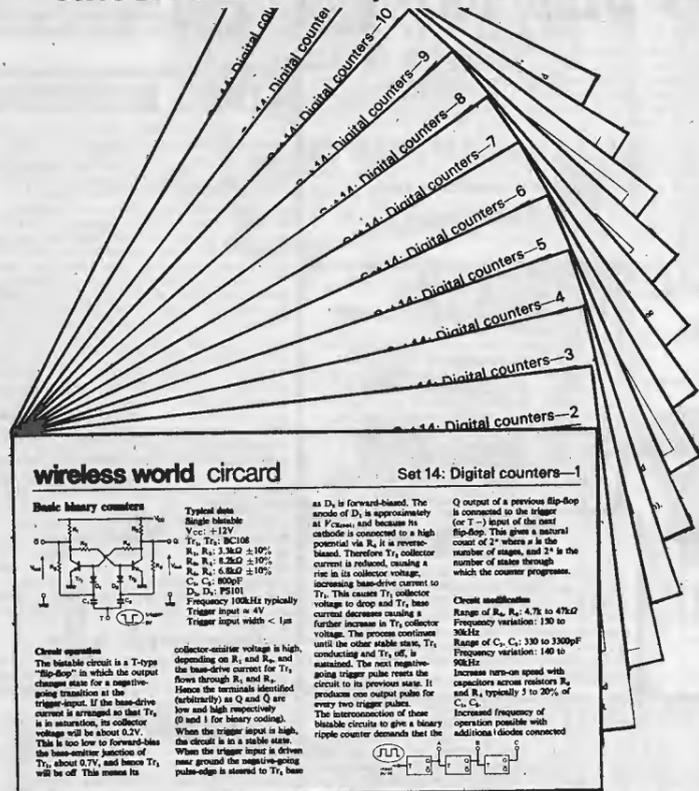
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**ELECTRONIC COMPUTER AND MANAGEMENT APPOINTMENTS LIMITED** (1926)  
 148-150 High St., Barkway, Royston, Herts SG8 8EG.

## Junior Radio Officers

The Royal Fleet Auxiliary has a number of vacancies for Junior Radio Officers. These appointments are for short term engagements of 6 months duration, (with the possibility of extension) and offer recently qualified personnel the opportunity to gain the required seetime.

Minimum qualifications: MRGC and DTI Radar Maintenance Certificate.  
 Apply in the first instance, by telephone to:— Dave Poynter, RFA Personnel Office, (Radio), on 01-385 1244 ext. 3041.

**ROYAL FLEET AUXILIARY RFA** (2071)



## SENIOR ENGINEER

ENG/OB Maintenance

**Salary in the range £14,000-£17,800**

Independent Television News Limited has a vacancy for a Senior Engineer in their ENG/OB Maintenance Section at ITN House, London W1.

The successful candidate would join the specialist team responsible primarily for the maintenance of ENG equipment including Sony BVU series U-matics, Sony BVP330 cameras, TBCs and associated portable equipment. The section is also responsible for the long-term maintenance of our two camera OB unit.

The work may occasionally involve travel with ENG teams to remote locations.

Previous maintenance experience with U-matic equipment and/or lightweight cameras is essential.

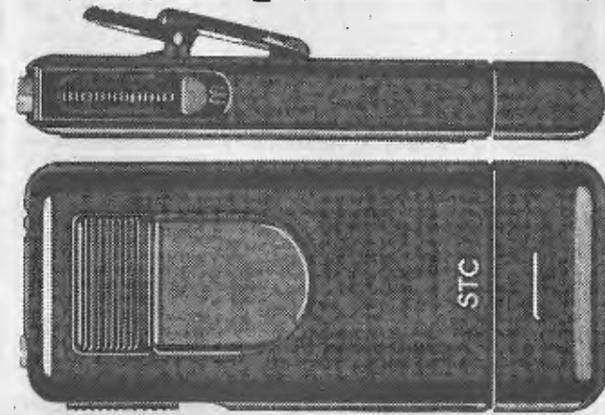
Generous pension scheme, free life assurance.

Please telephone the Personnel Office on 01-637 3144 quoting reference number 303005. (2074)

# ELECTRONICS PROFESSIONALS

## The 1980s herald a new era in personal communications development.

With a respected pedigree of world leadership in advanced communications, STC are breaking new ground in the exciting and fast expanding field of personal communications. Achievements in this high technology area have already earned recognition with the 1982 Design Council Award for the STC Radiopager — one of the smallest and most highly attractive pagers on the market. We are determined to build on this success by taking our micro engineering expertise through into a new era of personal communications.



To continue innovation in this challenging field, we intend to strengthen our successful team by appointing a select number of talented professionals.

Our salary package is first-class and is further enhanced by a full range of valuable benefits including life, health and pension schemes, and, where appropriate, generous assistance with relocation to our location on the fringe of London's northern green belt. Future career prospects are excellent with progression being on a 'dual ladder' basis, where both technical and management abilities achieve equal recognition.

So join the STC team and help lead our drive into a new era of personal communications technology. For more information, please write or better still telephone: **Vaughan Hartridge,**

**Standard Telephones and Cables plc,**  
 Oakleigh Road South, New Southgate  
 N11 1HB. Tel: 01-368 1234, ext. 2215.

## We're determined to turn state-of-the-art theory into world-class quality products. Join our team now!

### Section Head

a demanding role for a mature and very determined professional to lead a design team creating our next generation of successful products. You'll need to be a senior electronic engineering professional who has progressed through to management via technical achievement.

### Senior Software Engineer

to be closely involved in all aspects of new product

development from planning through to realisation of software. A minimum of 5 years' experience with microprocessors and software engineering is essential.

### Senior Digital Engineer

who must be capable of taking a lead responsibility for the hardware design of the digital section of our product range. A broad experience of digital circuit design including microprocessors is essential.

**STC Telecommunications**

(2085) **STC**

## CUT THIS OUT!

Clip this advert and you can stop hunting for your next appointment. We have a wide selection of the best appointments in Digital, Analogue, RF, Microwave, Microprocessor, Computer, Data Comms and Medical Electronics and we're here to serve your interests. Call us now for posts in Design, Sales, Applications or Field Service, at all levels from £6,000-£16,000.



11 Westbourne Grove, London W2. Tel: 01-229 9239. 1935



## TRAINEE BROADCAST ENGINEERS

Vacancies exist at ITN for Engineering Trainees which could provide the opportunity to start a career in Broadcast Television Engineering with ITV.

Firstly, a firm interest in pursuing a career in the technical branch of broadcasting is necessary.

Then you should have completed or expect this year to complete, theoretical training in Electronic Engineering with a bias towards Television or Audio applications. Qualifications most suitable are T.E.C. Higher Technical Diploma, T.E.C. Higher Technical Certificate or the HND/HNC equivalent.

Initially, you would be involved in a familiarisation period by a rotational attachment to our four maintenance areas and the Projects Department. This lasts for up to 15 months.

After successful training you would be employed on the maintenance or operation of a wide range of broadcast equipment in our Central London Studios near Oxford Circus, from which the ITN national news programmes are networked.

Successful applicants will join ITN in early September, 1983. Starting salaries would lie within the range of £5,642 (at 18) rising to £7,109 at age 20.

If you have the qualifications and the drive to work with us in a busy lively environment, then call us on 01-637 3144 or write to:

The Personnel Manager  
Independent Television News Limited  
ITN House  
48 Wells Street  
London  
W1P 4DE

for an application form quoting reference number 0476007.

(2054)

## BROADCAST ENGINEER

Required by the Broadcast Division of The Services Sound and Vision Corporation, who provide broadcast television and radio services to H.M. Forces and their dependants abroad.

Candidates (preferably aged 22-35) should be educated to HND/HNC standard in electrical or electronic engineering and have work experience in the broadcasting industry.

Their work (mostly overseas) includes the installation, operation, repair and maintenance of the full range of professional radio studio equipment and MW and VHF broadcast transmitters.

A tax free salary in the range of £7,914 to £9,994 is paid overseas, plus generous tax-free overseas allowances and other fringe benefits. There are promotion prospects to higher grades, and opportunities for training and transfer to the Television Division.

Please apply in writing to:

Personnel Manager,  
The Services Sound and Vision Corporation  
Chalfont Grove, Gerrards Cross  
Bucks SL9 8TN

(2052)

## ADVANCED TELECOMMUNICATIONS:

careers with extensive scope at Cheltenham

Join the Government Communications Headquarters, one of the world's foremost centres for R & D and production in voice/data communications ranging from HF to satellite - and their security. Some of GCHQ's facilities are unique and there is substantial emphasis on creative solutions for solving complex communications problems using state-of-the-art techniques including computer/microprocessor applications. Current opportunities are for:

### Telecommunication Technical Officers

Two levels of entry providing two salary scales: £5980-£8180 and £8065-£9085

Minimum qualifications are TEC/SCOTEC in Electronics/Telecommunications or a similar discipline or C & G Part II Telecommunications Technicians Certificate or Part I plus Maths B, Telecommunications Principles B and either Radio Line Transmission B or Computers B or equivalent: ONC in Electrical, Electronics or Telecommunications Engineering or a CIE Part I Pass, or formal approved Service technical training. Additionally, at least four years' (lower level) or seven years' (higher level) appropriate experience is essential in either radio communications or radar, data, computer or similar electronic systems. At the lower entry level first line technical/supervisory control of technicians involves "hands-on" participation and may involve individual work of a highly technical nature. The higher level involves application of technical knowledge and experience to work planning including implementation of medium to large scale projects.

### Radio Technicians

£5232-£7450

To provide all aspects of technical support. Promotion prospects are good and linked with active encouragement to acquire further skills and experience. Minimum qualifications are a TEC Certificate in Telecommunications or equivalent plus two or more years' practical experience. Cheltenham, a handsome Regency town, is finely-endowed with cultural, sports and other facilities which are equally available in nearby Gloucester. Close to some of Britain's most magnificent countryside, the area also offers reasonably-priced housing. Relocation assistance may be available.

For further information and your application form, please write to

Recruitment Office  
GCHQ Oakley, Priors Road  
Cheltenham, Gloucestershire GL52 5AJ  
or phone 0242 21491, Ext. 2269.

(1998)



## CAPITAL APPOINTMENTS LTD

THE UK'S No. 1 ELECTRONICS AGENCY

If you have HNC/TEC or higher qualifications and are looking for a job in design, test, customer service, technical sales or similar fields:

Telephone now for our free jobs list  
We have vacancies in all areas of the UK  
Salaries to £15,000 pa

01-637 5551 or 01-636 9659  
(24 hours)

Or if you prefer send a FULL CV to:

CAPITAL APPOINTMENTS LTD  
29-30 WINDMILL STREET, LONDON W1P 1HG

(291)

# RF Engineers & Senior Engineers

Our Client is an internationally successful Company that you'll both know and respect. A world-renowned force in advanced communications products, they have a track record of technological innovation and commercial success that is second to none.

The Company's achievements in the fast expanding personal communications market are considerable - and their product range continues to receive wide acclaim - both in the market and also within the industry. Now to maintain this momentum of success, they intend to lead the way in developing the next generation of advanced, high technology personal communications products.

They therefore wish to strengthen their highly talented, integrated design and development teams by appointing several key Engineers - at Senior and Middleweight levels.

The need is for experienced professionals to become immediately involved in projects which will fully exploit the latest state-of-the-art technology in the ever-advancing field of circuit integration. You will initiate designs for large sections of a major project workload - and when you are ready for more responsibility, there are opportunities in both

project and man-management.

To be considered, you must have an HND/Degree in electronics together with between 2-7 years' experience in analogue circuit VHF/UHF design and application. A background in mobile, military or airborne radio would be an advantage - but most importantly, you must demonstrate the ability to liaise with related engineering disciplines, manufacturing and marketing.

We recognise that we are looking for a "rare breed" of Engineer - and the remuneration package will reflect the importance of your role. Initial salaries will be highly attractive and individually negotiable, further enhanced by a full range of benefits. As far as the future is concerned, there are opportunities for very positive career progression within this successful and dynamic organisation.

Find out the full story about the Company of the future in RF technology. Please telephone Kevin Long on 01-636 5538 in complete confidence or write with a c.v. to him at: Moxon Dolphin & Kerby Ltd., 178-202 Great Portland Street, London W1N 5TB, quoting ref: KL/980/W.

## In the race to develop the next generation of personal communications products...

MOXON  
DOLPHIN  
& KERBY LTD

## ...Join the Company that will win!

(2084)

Royal Marsden Hospital,  
Fullham Road, London SW3

## Medical Physics Technician

MPT2

required in the Physics and Radiotherapy Departments. The appointed person will be responsible for the supervision of a pleasantly situated, well-equipped electronics workshop and the maintenance and service of an interesting variety of radiotherapy equipment.

The Department has 3 cobalt treatment machines, 150kv and 300kv X-ray units, a Philips 10mv linear accelerator and a simulator. Current developments include the installation of a Philips 5mv linear accelerator and caesium Selectron unit.

Applicants should hold ONC, HNC or similar qualification in electrical engineering or (preferably) in electronics, and have relevant technical experience particularly with Philips linear accelerators. To be appointed on to the MPT2 scale applicants should have served at least 2 years as MPT3 or equivalent. Salary scale from 1st April 1983 £8,383-£10,209 per annum.

Application form and job description available from the Personnel Department, Royal Marsden Hospital, at the above address. Tel: 01-352 8171 Ext. 446/447.

(2053)

## VIDEO ENGINEERS

Rediffusion Consumer Manufacturing Ltd is seeking intermediate and senior video engineers with OND, HND or similar qualifications, together with a knowledge of analogue and digital circuits, to join a small team working on a wide variety of projects associated with video cassette recorders, video cameras, disc players, colour TV receivers and monitors.

In addition to analysis of performance and long term reliability factors, assessment reporting is an important part of the team's function and the ability to express oneself verbally and in writing is essential.

Our laboratories are situated at Chessington within easy commuting distance of the Surrey countryside.

Attractive salaries and the usual big company benefits are offered to suitably qualified and experienced engineers. If you believe you can make an effective contribution to our future video projects please write to or phone:

Mr Harry Brearley  
Rediffusion Consumer Manufacturing Ltd.  
Fullers Way South  
Chessington, Surrey KT9 1HJ  
Telephone: 01-397 5411

REDIFFUSION

(2070)

## Civil Aviation College (Gulf States) Doha, Qatar

requires for September 1983:

### INSTRUCTOR AVIATION ELECTRONICS

University Degree and Professional qualifications in Aviation Electronics, qualified and experienced in installation and maintenance of Modern Radio Systems  
Must have minimum ten years' experience with three years' instructional experience at an ICAO recognised Training Centre.

Salary and Allowances up to US\$3400 per month

Applications to:

**The Principal  
Civil Aviation College (Gulf States)  
P.O. Box 4050  
Doha  
State of Qatar**



(2088)

#### UNIVERSITY OF ABERDEEN

Department of Bio-Medical  
Physics and Bio-Engineering

### ELECTRONIC OFFICER

required for well-equipped Electronics Section (staff 15) of internationally known Department to be associated with design, servicing and maintenance of modern medical electronic equipment in hospitals and laboratories. The Officer will be expected to guide technicians and help actively research in bio-medical applications of electronics. Additional experience desired in one or more relevant areas of instrumentation — eg vacuum, lasers, high voltage, high frequency.

Salary within the Grade 1A scale for Other Related Staff (£3,375-£11,105 per annum) with appropriate placing.

Further particulars and application forms from The Secretary, The University, Aberdeen, with whom applications (two copies) should be lodged by 10 May, 1983.

(2072)

### Manor Studios

Require a full-time

### MAINTENANCE ENGINEER

Based in Oxfordshire, duties will include work at the Manor Studio and on location with the mobile. For details please ring:

**PAUL WARD — 08675 77551**  
(2067)

### THIS IS ENGINEERING PAR EXCELLENCE

An opinion of our client company shared by the highest in the land — yes, a Queen's Award winner 1982

### DESIGN ENGINEERS

are required to augment this exceptionally talented team who have achieved the following:

Launched a video graphic product for broadcast TV in 1978 which still has no rival in the British or European television industry. Not surprising — modern bit slice technology designed for maximum reliability, rugged environment and artistic appearance.

Designed a second generation product which has burgeoned into a whole family of new products including devices for graphic animation. Teletext peripherals, encoding and data logging products for future TV applications.

Have the next generation of products in the pipeline — confidential of course — however, one look around the laboratory and you can bet they will be one of the first into 32 bit micros and mega-byte rams.

Created an extremely pleasant working environment and attractive financial package for their staff. Salary is above average, also BUPA, life assurance and subsidised canteen.

Graduates with relevant experience, don't sit around, ring or send your C.V. to their chosen agents.

## Charles Airey Associates

Tempo House, 15 Falcon Road, Battersea, London SW11 2PJ  
Telephone: 01-223 7682 or 228 6294 (2061)

### BORED ?

Then change your job!

**1) Test Equipment Controller**  
Plan and procure test equipment and control a team of test equipment engineers. To £12,670 — Hants.

**2) Maintenance Engineer**  
Start an in-house test of communications equipment — then move to field service when fully conversant. To £8,000 + car — London.

**3) Service Engineer**  
Analogue and digital detection and alarm systems. Middx-Essex — to £8,000.

**4) Test Engineer**  
In-house work on modems and data communications systems. To £7,500 — Bucks.

**5) Service Personnel (RAF, RN, Army)**  
We have many clients interested in employing ex-service fitters and technicians at sites throughout the UK. Phone for details.

**6) £500 per week**  
We are paying very high rates for contract design and test engineers who have a background in RF, MICROWAVE, DIGITAL, ANALOGUE or SOFTWARE, at sites throughout the UK.

Hundreds of other Electronic and Computer Vacancies to £12,500

Phone or write:  
**Roger Howard, C.Eng. M.I.E.E., M.I.E.R.E.**  
**CLIVEDEN CONSULTANTS**  
87 St. Leonard's Road, Windsor, Berks.  
Windsor (07535) 58022 (5 lines) (1646)

### CLIVEDEN

#### UNIVERSITY OF YORK

Department of Electronics

Applications are invited for the post of

### Senior Technician

(GRADE 5)

in the central workshop of the new Department of Electronics. The workshop staff are responsible for the maintenance of electronic instruments and for the development and construction of electronic equipment for teaching and research purposes.

Applicants are expected to have an appropriate qualification and considerable experience of electronic engineering, preferably including computers. The salary scale is currently £6,009-£7,016 p.a.

Applications giving full details of age, education and experience, together with the names and addresses of two referees, should be sent to Mr D. Rymer, Assistant Bursar, University of York, York YO1 5DD by Tuesday, May 3, 1983. (2075)

#### INNER LONDON EDUCATION AUTHORITY

Learning Resources Branch  
Television Centre  
Thackeray Road  
Battersea SW8 3TB

### ENGINEER — ELECTRONIC MAINTENANCE

Salary range: (ST2) £7,035 to £7,974 plus £1,284 London Weighting Allowance.

The ILEA's Television Centre produces a wide range of educational programmes on video and audio cassettes. The Maintenance section numbers four persons and a vacancy has arisen for an engineer with a sound knowledge of the principles of colour television, and preferably a working experience of maintaining broadcast type TV equipment. Applicants must wish to specialise on the video side (cameras, vision mixers, telecine, etc.), and will receive appropriate training. An engineering degree, TEC or other equivalent qualifications are desirable.

Application forms from the Education Officer (EO/Estab. 1B), Room 365, The County Hall, London SE1 7PB. Please enclose a stamped and addressed foolscap envelope. Completed forms to be returned by May 4, 1983.

ILEA is an equal opportunities employer. (2066)

### RADIO ENGINEER

To work as a technical adviser with a Latin American organisation for education by radio, with 40 affiliated radio stations in 17 countries.

The engineer will initially be based in Quito, Ecuador and will later travel to radio stations in other countries. The job consists of planning and running training courses for local technicians in maintenance of mainly small, short and medium wave transmitters, aeriels and studios.

Applicants should have radio engineering experience, gained in a broadcasting environment: the post will demand skills in training people with non-technical backgrounds and in planning and improvising equipment. Spanish speakers especially welcome, but language training can be provided.

The post is initially for three years on a basic salary. Because of extensive travel, it is unlikely to suit applicants with families. CIIR will provide orientation and language training, insurance, air-fares and various allowances.

For a job description and application form, please send a brief cv to CIIR Overseas Programme, 22 Coleman Fields, London N1 7AF, quoting ref WW/1. (2087)

### Botswana

## Assistant Force Communications Officer

Up to £16,470 p.a. substantially tax-free

A challenging post with the Police in a democratic, multi-racial developing country in southern Africa.

Candidates, preferably aged between 30 and 45, must possess City and Guilds Part II or equivalent and have at least five years' experience in police or armed forces communications with HF, SSB and VHF (FM) communications equipment.

Duties include the maintenance, installation and fitting of communications equipment and the training of junior technicians for C & G examinations.

Benefits include free passages, generous paid leave, children's holiday visit passages and education allowances. Basic salary attracts 25% tax-free gratuity on completion of three year contract.

For further details and application form ring Linda Mitchell on 01-222 7730 extension 3714 or write quoting YX/1013/WW.

### Crown Agents



The Crown Agents for Oversea Governments  
& Administrations, Recruitment Division,  
4 Millbank, London SW1P 3JD (2081)

## Hospital Medical Equipment Technicians

C. £15,400\* Tax Free  
+ substantial benefits in Saudia Arabia

As a leading international healthcare company, staffing and managing several hospital projects in the Middle East, the efficient maintenance of medical equipment is a vital part of our operation. Consequently we are seeking additional male technicians with the following experience to join us at one of these hospitals in the Kingdom of Saudi Arabia.

You must hold an HNC in Medical Electronics or Electronic Engineering and have at least 3 years' post qualification experience of hospital medical equipment including microprocessor controlled patient monitoring or X-ray equipment.

The substantial tax free salary offered (\*paid in US dollars and converted in this instance at a rate of US\$ 1.55=£1.00) is supported by the wide range of benefits outlined below:

### The Whittaker Benefits Package

- \* Choice of 1 or 2 year contracts
- \* 7 weeks holiday
- \* Mid-year holiday allowance
- \* Return air fare
- \* Comprehensive insurance cover
- \* Free local transport
- \* End-of-contract bonus
- \* Storage allowance
- \* Free recreation facilities
- \* Free, furnished, fully-equipped, air-conditioned accommodation.

You'll be ideally placed to make the most of your holidays, travelling even further afield—to Nairobi, Singapore, Hong Kong or Bangkok for example.

If you hold a UK or Irish passport and are interested in a 1 or 2 year renewable, single status contract, phone Irene Cooper or Michelle Chudley on 01-434 1081 reversing the charges and quoting ref: E360. Alternatively, write to Whittaker Life Sciences Limited, Freepost 35, London W1E 5QZ.

DEDICATED TO A WORLD OF HEALTH  
**Whittaker**  
LIFE SCIENCES LIMITED

(2093)

## TRAINEE ASSISTANT PICTURE EDITORS Television News

Assistant Picture Editors will work with film and ENG on all programmes produced by Television News. Trainee Assistant Picture Editors will be given a comprehensive training to enable them to progress to Assistant Picture Editors and eventually to compete for posts as Picture Editors. Most duties involve shift working, including nights.

Candidates with an Arts or Engineering based background and at least 'O' level standard in Maths, English and a Science subject, preferably Physics, will be considered and they will be required to demonstrate an ability and potential to undertake the necessary technical training. Higher qualifications in either Arts or Science subjects would be an advantage. Candidates should be able to work under pressure, react quickly to changing circumstances and have normal hearing and colour vision, with an informed and lively interest in News and Current Affairs.

Initial salary will be £6734 which includes a continuing shift allowance. (General salary review due in April). Based West London. Relocation expenses considered.

Contact us immediately for application form (quote ref. 1283/WW and enclose s.a.c.): BBC Appointments, London, W1A 1AA. Tel. 01-580 4468 Ext. 4619.

We are an Equal Opportunities employer



## A NUMBER OF THINGS YOU SHOULD KNOW ABOUT COMMUNICATIONS TECHNOLOGY

Those 'things you should know' are the opportunities available to people with experience in high technology areas of the communications industry. Below are a sample. Telephone Paul Hecquet on Lewes (07916) 71271 to discuss these and many more.

- |   |                   |                      |
|---|-------------------|----------------------|
| <b>Video (Image Processing) Design Engineer</b>   | <b>c £15,000</b>  | <b>Home Counties</b> |
| Experience in fields such as slowscan would be desirable. Ref: 3/80.                                  |                   |                      |
| <b>RF Senior Development Engineer</b>   | <b>c £11,000</b>  | <b>West Country</b>  |
| Design and Development on advanced range of signal processing (High frequency) components. Ref: 4/13. |                   |                      |
| <b>Cabel TV Systems Engineer</b>  | <b>c £16,000+</b> | <b>Home Counties</b> |
| To work on cable TV proposals involving total systems (turnkey) design. Ref: 5/79.                    |                   |                      |
| <b>RF Circuit Design</b>  | <b>c £9,000</b>   | <b>Home Counties</b> |
| Design and Development RF circuitry for commercial mobile radio systems. Ref: 3/28.                   |                   |                      |
| <b>RF/ATE Group Manager</b>   | <b>c £20,000</b>  |                      |
| Responsible for Design/Development and manufacture of RF/ATE. Ref: 6/48.                              |                   |                      |

(2079)

## The Electronics Recruitment Company

Temple House  
25/26 High Street, Lewes  
East Sussex BN7 2LU  
Tel: Lewes (07916) 71271

### SOUTHERN DERBYSHIRE HEALTH AUTHORITY MANOR HOSPITAL, UTTOXETER ROAD DERBY DE3 3NB ENGINEERING ELECTRONICS TECHNICIAN III

To carry out maintenance, repair and modification of electronic equipment used in medical and engineering applications. The successful applicant will be expected to undertake necessary training to enable him/her to maintain medical gas equipment. A current driving licence and possession of a car are essential. Applicants should be qualified to O.N.C. or equivalent standard and have at least three years' experience in a similar position of responsibility.

Application form and further details from: Mr. D. Hargreaves, Assistant District Works Officer (Engineering). (Ref. No. 895).

(2057)

### Filter Engineer

An opportunity has arisen for a professional filter engineer experienced in the specification and design of complex passive filters. Experience in active and SAW filters or other areas of electronics would be advantageous. This is a permanent, senior position in an expanding company.

Apply to:  
WIRELESS WORLD  
BOX NO. 2077  
for further details

(2077)

### Broadcast/ Data Comms Engineers

HNC standard for both permanent and contract positions.

Tel. Camberley 0276 62466  
Jenrick (agy) (2083)

### LOGEX ELECTRONICS RECRUITMENT

Specialists in Field & Customer Engineering appointments, all locations and disciplines.

Logex House, Bursleigh, Stroud  
Gloucestershire GL5 2PW  
0453 883264 & 01-290 0267  
(24 hours)

### Services

The Professional CV people

- ★ Quick
- ★ Efficient
- ★ Confidential

We prepare top-quality résumés at a price you can afford

For further information write/phone:  
CV Services, 10 Wilton Road, Hitchin,  
Herts SG5 1SS. Tel: Hitchin (0462) 31836  
(2073)

R & D OPPORTUNITIES. Senior level vacancies for Communications Hardware and Software Engineers, based in West Sussex. Competitive salaries offered. Please ring David Bird at Rediffusion Radio Systems on 01-874 7281. (1162)

## Telecommunications Technicians

### Up to £9403

The posts available are varied, but broadly they fall into 2 groups at 3 different locations.

### HANSLOPE PARK (MILTON KEYNES) and CENTRAL LONDON

for installation, maintenance and other work associated with HF communications equipment, VHF, UHF and microwave links and associated test equipment; teleprinters, telephone subscribers' apparatus, PMBXs, PAXs, PABXs and ancillary equipment including that using analogue and digital techniques and voice frequency telegraph.

### CROWBOROUGH, SUSSEX

for maintenance and operation of high power, medium and short wave broadcasting transmitters and associated equipment.

Applicants should normally have 4 years' relevant experience, and must hold one or more of the following:

- ★ ONC in Engineering (with pass in Electrical Engineering 'A')
  - ★ ONC in Applied Physics
  - ★ TEC/SCOTEC certificate
  - ★ City & Guilds Telecommunications Technicians Certificate Part II (Course No. 271) or Part I plus Maths 'B', Telecommunications Principles 'B' and one other subject.
  - ★ a pass in the Council of Engineering Institutions Part I examination
  - ★ an equivalent or higher relevant qualification.
- Ex-Service personnel who have had suitable training and at least 3 years' appropriate service (as Staff Sergeant or equivalent) will also be considered.

Salary: £5983-£8183; London £1220 more. Starting salary may be above minimum for those with additional relevant experience. Promotion prospects are good.

Relocation assistance may be available.

For an application form (to be returned by 19 May) write to: Foreign & Commonwealth Office, Hanslope Park, Hanslope, Milton Keynes MK19 7BH, or telephone Milton Keynes (0908) 510444 Ext. 232. Please quote reference YHU/TT2/83.

Foreign & Commonwealth Office

(2065)

## Telecommunications Engineer

### £9,504-£10,071

The responsibilities will cover the design, construction and installation of purpose-built telecommunications equipment and modifications to installed equipment subject to CAA approval. The successful applicant will also be required to assist other members of the Telecommunications Section in the maintenance and repair of equipment within the Telecommunications Department.

Applicants should be educated to at least HNC or equivalent in Electronics and have a minimum of five years' practical experience in fields including RF, AF and Digital Techniques.

Generous relocation expenses are payable in appropriate cases and temporary housing accommodation may be available.

Application forms, returnable by May 6th, 1983, may be obtained from the Personnel Department, Town Hall, Luton LU1 2BQ. Tel: Luton 31291 ext 2300. (2090)



# Electronics Design Engineers

## Communications

R/F VHF UHF Systems  
R/F HF Systems  
Microwave Equipment  
Analogue Digital Circuitry  
Message Circuit Switching  
Cryptographic Systems

Marconi Space and Defence Systems, Communications Division, are rapidly expanding their civil and military projects. Additional experienced staff qualified to PhD/Degree/HND/HNC are required at all levels of responsibility for software/hardware development in the above areas. Our salary scales match the high standards of qualifications, experience and ability demanded. We offer a comprehensive range of benefits together with relocation assistance if required.

Phone Portsmouth 674019 for further information and an application form. Alternatively, you can write to Jack Burnie, Marconi Space and Defence Systems Limited, Browns Lane, The Airport, Portsmouth, Hants, quoting ref: BL 25.

(All posts are open to men and women)

**Marconi**  
Space & Defence Systems



## EVTR is looking for a young Video Engineer

EVTR is a broadcast television facilities company specialising in the use of computer editing equipment.

We need a qualified electronics person who is willing to work a shift system and gain experience of broadcast, video tape recording and operational engineering.

Please telephone Andy Thompson  
on 01-631 4421  
21 Great Tichfield Street  
London, W.1

(2063)

### ARTICLES FOR SALE

Word Processor Clearance Sale. BDP/Quine Daisy-wheel printer, 2 discs; £595. Adler SE2000-Golfball printer, single disc; £450. Kalle Infortec 7000-Golfball printer. Single tape; £350. All + VAT. Autotype, Haywards Heath (0444) 414484 money off voucher). 23 Irwin Drive, Horsham, RH12 1NL. No callers. (2017)

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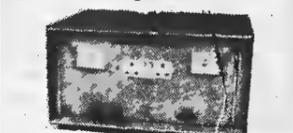
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