

ason's Greetings

DECEMBER 1988

\$2.50

HAM RADIO



ICOM

IC-735 HF Transceiver



'MOST RELIABLE HF'

"Of all the possible radios, I chose the ICOM IC-735 for my CQWW QRP world record attempt."

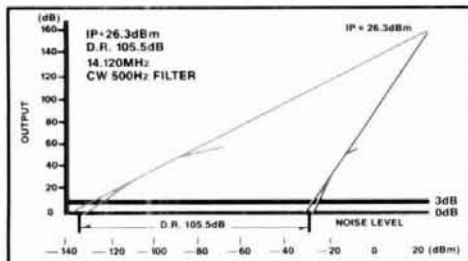
Danny Eskenazi, K7SS, World High QRP Score
 -1987 CQWW SSB (PJ2FRI)
 -1986 CQWPX SSB (K7SS WH6)
 -1986 ARRL DX PHONE & CW (K7SS KH6)

ICOM's IC-735 is the world's most popular HF transceiver. With the highest performance, smallest size, and best customer satisfaction of any HF transceiver, the IC-735 is the winner's choice for fixed, portable, or mobile operations.

- **Field Proven 100W Transmitter** with 100% duty cycle. Proudly backed with ICOM's full one-year warranty.
- **105dB Dynamic Range Receiver** includes passband tuning, IF notch, adjustable noise blanker, and semi or full CW QSK.
- **Conveniently Designed.** Measures only 3.7"H by 9.5"W by 9"D.



- **Optional AH-2 Automatic Tuning Mobile Antenna System** covers 3.5MHz-30MHz and tracks with the IC-735's tuned frequencies.
- **All HF Amateur Bands and Modes** plus general coverage reception from 100KHz-30MHz.



- **12 Tunable Memories** operate and reprogram like 12 separate VFO's. Supreme flexibility!

Additional Options: SM-10 graphic equalized mic. PS-55 AC power supply, AT-150 automatic antenna tuner for base operation.

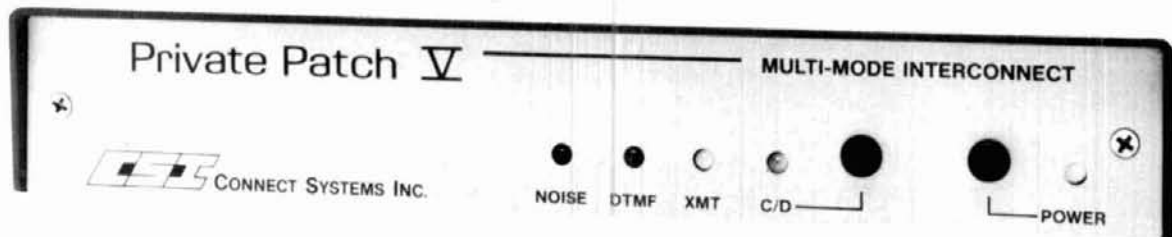
ICOM's IC-735... a proven winner for reliable worldwide HF communications. See it today at your local ICOM dealer.

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First in Communications

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Customer Service Hotline (206) 454-7619
 3150 Premier Drive, Suite 126, Irving, TX 75063
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 ICOM CANADA, A Division of ICOM America, Inc.,
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 All stated specifications subject to change without notice or obligation. All ICOM radios significantly exceed FCC regulations limiting spurious emissions. 735188.
 *Final contest results pending.

FOUR user selectable operating modes and a 90 number autodialer make Private Patch V the ONLY choice!



SELECT AN OPERATING MODE USING THE BUILT-IN KEYBOARD . . .

1. SIMPLEX SAMPLING PATCH

Private Patch V achieves a level of sampling patch performance unobtainable in any other product. Crucial to performance is the noise squelch filter. Compare our five pole filter to the competition's two pole filter. Advanced software algorithms perform noise correlation tests which result in greater useable range than the competition. Nine selectable VOX enhancement ratios allow you to vary performance from straight sampling to highly VOX enhanced. (sampling rate decreased while the land party is speaking). The mobile is in full control and can break-in at any time.

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VOX mode offers superb simplex operation with any radio, including synthesized and relay switched models. VOX mode has other advantages too. 1. A linear amplifier can be used to extend straight simplex range. 2. You can operate through any remotely located repeater to greatly extend range. 3. If desired you can connect Private Patch V to the MIC and speaker jack of your radio. NO INTERNAL CONNECTIONS ARE REQUIRED. Control is maintained automatically with built-in dial tone detection, busy signal detection and fully programmable activity and time out timers. An optional electronic voice delay board eliminates first word clipping with slow switching radios.

3. DUPLEX PATCH

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TH-315A
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Kenwood brings you the greatest hand-held transceiver ever! More than just "big rig performance," the new TH-215A for 2 m, TH-315A for 220 MHz, and TH-415A for 70 cm pack the most features and the best performance in a handy size. And our full line of accessories will let you go from hamshack to portable to mobile with the greatest of ease!

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- 5, 2.5, or 1.5 W output, depending on the power source. Supplied battery pack (PB-2) provides 2.5 W output. Optional NiCd packs for extended operation or higher RF output available.
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- Easy memory recall. Simply press the channel number!
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- Priority alert function.
- Monitor switch to defeat squelch. Used to check the frequency when CTCSS encode/decode is used or when squelch is on.



- Large, easy-to-read multi-function LCD display with night light.
- Audible beeper to confirm keypad operation. The beeper has a unique tone for each key. DTMF monitor also included.
- Supplied accessories: Belt hook, rubber flex antenna, PB-2 standard NiCd battery pack (for 2.5 W operation), wall charger, DC cable, dust caps.



Optional Accessories:

- PB-1: 12 V, 800 mAh NiCd pack for 5 W output
- PB-2: 8.4 V, 500 mAh NiCd pack (2.5 W output)
- PB-3: 7.2 V, 800 mAh NiCd pack (1.5 W output)
- PB-4: 7.2 V, 1600 mAh NiCd pack (1.5 W output)
- BT-5 AA cell manganese/alkaline battery case
- BC-7 rapid charger for PB-1, 2, 3, or 4
- BC-8 compact battery charger
- SMC-30 speaker microphone
- SC-12, 13 soft cases
- RA-3, 5 telescoping antennas
- RA-8B StubbyDuk antenna
- TSU-4 CTCSS decode unit
- VB-2530: 2m, 25 W amplifier (1-4 W input)
- LH-4, 5 leather cases
- MB-4 mobile bracket
- BH-5 swivel mount
- PG-2V extra DC cable
- PG-3D cigarette lighter cord with filter



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KENWOOD U.S.A. CORPORATION
2201E Dominguez St., Long Beach, CA 90810
P.O. Box 22745, Long Beach, CA 90801-5745

Complete service manuals are available for all Kenwood transceivers and most accessories. Specifications and prices are subject to change without notice or obligation.

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DECEMBER 1988

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FEATURES

9 A Simple Direct Conversion Receiver

Rodney A. Kreuter, WA3ENK

19 The Weekender: Build This Simple L-C Checker

Jack Najork, W5FG

22 Ham Radio Techniques: New Zealand, Maui, and the Solar Cycle

Bill Orr, W6SAI

29 Structural Evaluation of Yagi Elements

Dick Weber, K5IU

51 Formatted Display of Packets Using KISS

Michael Pechura, WA8BXN

60 Decoding Data Signals

James A. Sanford, WB4GCS

75 A Homebrew Tuning Dial

John Pivnichny, N2DCH

83 Practically Speaking: Overview of Operational Amplifiers: Part 2

Joe Carr, K4IPV

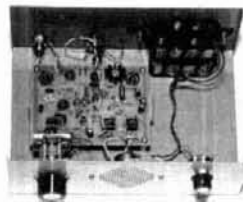
88 The Weekender: Get the Most from Your NiCds

W.C. Cloninger, Jr., K3OF

117 Elmer's Notebook: SSB Basics — Receiving the Signal

Tom McMullen, W1SL

Joe Reiser's column returns next month.



WA3ENK, page 9



THE WEEKENDER

W5FG, page 19

K3OF, page 88

See page 78 for the winners of
October's handheld radio
contest.

DEPARTMENTS

Backscatter	4	Short Circuits	107
Comments	6	DX Forecaster	110
Ham Notebook	26	Flea Market	118
New Products	59, 70, 104, 125	Advertiser's Index	126
Ham Mart	106	Reader Service	126

Special thanks to Hans Evers, PA0CX, for all his great covers this year.

BACKSCATTER

A year of change at HAM RADIO.

What fosters a good relationship between a magazine and its readers? When I arrived here a little over a year ago, I asked myself that question. I decided that, first, I had to get to know you. I needed to find out what Amateur Radio, in general, and HAM RADIO Magazine, in particular, meant to you. I began reading letters, manuscripts, notes on renewal notices, old surveys — anything I could get my hands on. I met you at shows in Dayton and Boxborough. What I found was an incredibly diverse group of people — teachers, accountants, machinists, doctors, engineers, pilots, bank tellers, journalists, students, homemakers, retired persons (the list goes on and on) — all bound together by a love for Amateur Radio. And even within the hobby itself, there is something for everyone. Whether you build, contest, do public service work, or just like to get on the radio and talk, you can find a niche in this great hobby. I suddenly noticed antennas I'd never seen before in my neighbors' backyards, a ham radio communications post at a local road race I ran in, callsigns on license plates — Amateur Radio is everywhere and a very important part of lots of lives!

How does HAM RADIO Magazine fit into your lives? There was a common theme in all your correspondence to us. You liked the technical flair of the magazine, but found many of the articles were dry, complicated, or just plain too long. You wanted more construction projects, weekenders, and shorter technical pieces that explained the theory behind the idea in a more concise fashion. But, you didn't want HAM RADIO to become "just another contest magazine." You liked what we were; you simply wanted some refinements.

After the Dayton Hamvention, the editorial staff got together to decide how to best meet your requests. In September we launched our first "new" HAM RADIO issue. We filled it with the kinds of articles you wanted to see (Weekenders, ham notes, projects, technical pieces), gave it a different look, and included evaluation cards for your comments. Your response to each new issue has been tremendous; it has given us a yardstick by which we can judge our performance. Without you, we could not have effected this change. With you, and your continued support, we will continue to grow.

Because our changes have been so well received, we'll carry them into the future. In the months to come you can look forward to pieces on ATV, digital voice, and new antenna designs. And, for you homebrew buffs, January brings our first construction issue.

Of course, our ability to deliver the kind of magazine you want to read depends not only on your constructive criticisms, but on the fine manuscripts you submit. You are our writers as well as our readers, and we'd love to help you share what you've built or learned with your fellow Amateurs. If you don't know how to get started, write for our author's guide; it's got lots of helpful hints. C'mon, what are you waiting for?

It's been a long year. A year of change — but positive change. You've been with us through it all. We thank you and look forward to a long happy relationship with you — our readers and friends.

Terry Northup
Managing Editor

P.S. Thought you'd like to know that I too have succumbed to the lure of Amateur Radio. I passed my Novice test and am waiting for my license to come. Hope to see you soon on the Novice bands!

KA1???

Correction: In our November editorial, "A potential danger," the National Career Institute was listed as a group concerned about the effects of electromagnetic radiation. The reference should have read National Cancer Institute. *Ed.*

**Happy Holidays from
all of us at Ham Radio**

KENWOOD

...pacesetter in Amateur Radio

Good
for Satellite
Digital QSOs

Matching Pair

TS-711A/811A VHF/UHF all-mode base stations

Look for
FUJI
and
PHASE III-C

The TS-711A 2 meter and the TS-811A 70 centimeter all mode transceivers are the perfect rigs for your VHF and UHF operations. Both rigs feature Kenwood's new Digital Code Squelch (DCS) signaling system. Together, they form the perfect "matching pair" for satellite operation.

- **Highly stable dual digital VFOs.** The 10 Hz step, dual digital VFOs offer excellent stability through the use of a TCXO (Temperature Compensated Crystal Oscillator).
- **Large fluorescent multi-function display.** Shows frequency, RIT shift, VFO A/B, SPLIT, ALERT, repeater offset, digital code, and memory channel.
- **40 multi-function memories.** Stores frequency, mode, repeater offset, and CTCSS tone. Memories are backed up with a built-in lithium battery.



- **Versatile scanning functions.** Programmable band and memory scan (with channel lock-out). "Center-stop" tuning on FM. An "alert" function lets you listen for activity on your priority channel while listening on another frequency. **A Kenwood exclusive!**
- **RF power output control.** Continuously adjustable from 2 to 25 watts.

- **Automatic mode selection.** You may select the mode manually using the front panel mode keys. Manual mode selection is verified in International Morse Code.
- **All-mode squelch.**
- **High performance noise blanker.**
- **Speech processor.** For maximum efficiency on SSB and FM.
- **IF shift.**
- **"Quick-Step" tuning.** Vary the tuning characteristics from "conventional VFO feel" to a stepping action.
- **Built-in AC power supply.** Operation on 12 volts DC is also possible.
- **Semi break-in CW, with side tone.**
- **VS-1 voice synthesizer (optional)** More TS-711A/811A information is available from authorized Kenwood dealers.



Optional accessories.

- IF-10A computer interface
- IF-232C level translator
- CD-10 call sign display
- SP-430 external speaker
- VS-1 voice synthesizer
- TU-5 CTCSS tone unit
- MB-430 mobile mount
- MC-60A, MC-80, MC-85 deluxe desk top microphones
- MC-48B 16-key DTMF, MC-43S UP/DOWN mobile hand microphones
- SW-200A/B SWR/power meters:
 - SW-200A 1.8-150 MHz
 - SW-200B 140-450 MHz
- SWT-1 2-m antenna tuner
- SWT-2 70-cm antenna tuner
- PG-2U DC power cable

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COMMENTS

Good news and bad news

Dear HR:

Just received the September 1988 issue of *HAM RADIO* magazine an hour ago. Naturally, I have not had time to go through it in great detail, but I like what I see and like it so much that I am willing to extend my subscription for another three years.

Now for the bad news. The printing job in my issue leaves much to be desired. Many of the pages have the material printed so close to the edge of the page that a slim portion of the text and advertising is cut off and missing. I assume this is a one-time problem.

Enclosed is my evaluation card. Keep Bill Orr's column coming. His writings are usually the first place to which I open your magazine. I have been a fan of his since the days of his antenna articles featuring Pendergast in the small-format CQ magazines.

**Lee G. Andreas, N9BDL,
Lake Tomahawk, Wisconsin
54539-9500**

Advice for the novice

Dear HR

Can't remember when I wrote a letter to the editor but Marty wrote an editorial (Reflections) in the August issue that I take exception to. He was commenting on the high cost of equipment to get the Novice started, and asking us to dig out the old stuff that is collecting dust to give them a start.

Have we forgotten that a one-tube crystal oscillator is a good CW transmitter? And, a two-tube regenerative receiver (or a transistor and op amp) make a compatible receiver?

We are doing an injustice to the young people when we try to train them to be appliance operators rather than giving them an introduction to the technical world and allowing them to enjoy communications with equipment they've constructed. Many of us have enjoyed careers as electronics engineers because we built our first equipment, and we built it because we could not afford the complete receivers and transmitters. If the beginners don't experience the pleasure of construction, how will they ever know?

If you really want to help the Novice, don't give them a radio, give them help in constructing a radio and a good antenna.

When the old timers get together, they don't talk about their first contacts without going into intricate detail about the design of their first hay-wired radio. Forty years from now, the Novice of today won't even remember which box he bought first.

**Ted Hart, W5QJR, Melbourne,
Florida 32902**

Handling traffic—a challenge

Dear HR

With regard to Mr. Harold P. Morgan, WDOP's letter in the July, "Comments", Ham Radio Magazine, I would like to say that I too am in complete agreement with Mr. Morgan. My situation is only somewhat different, for I am somewhat of a traffic handler.

Traffic is a challenge to me, in whetting my skills to enable me to receive a message, under the worst possible conditions, and to achieve the highest possible rate of accuracy. To take a piece of traffic from a station that is in the noise level, or below, and to have as close to 100-percent accuracy, is the name of the game for me.

Then, along comes our friend with the brand new super-duper, whiz bang, synthesized whats-it, and his Hakensak 5-PW amplifier, blasting the air waves with 3 or 4 kw, running up and down the band, with the key locked down; not just once or twice. No, he's got to run for it at least a half dozen times, before he qualifies. For what, I have yet to determine. And if, after all of this, you have anything left of your already diminishing hearing (having had the phones on, the bandwidth screwed down, and the volume up as high as you could stand it) you're just lucky as all get out.

I take exception to Mr. Morgan's, "wanting to hang them by their thumbs." While this just might keep them from reaching the key, and the VFO knob at the same time, it is quite doubtful that they would have learned anything from the experience. Given the fact that they have an extremely low I.Q. (they have already told this to the whole world) perhaps they need additional protection, namely from themselves. Perhaps an 8 or 9-foot square room, with lots of padding on the floor and walls, and a nice strong door, made from 3 inch thick planks, solidly set into the walls, would be appropriate.

I too have a chart, at the operating position, showing the dial setting for my antenna tuner for every 50 kHz, made some years ago during poor band conditions. With this chart, I am able to set-up a frequency, and not have my VSWR exceed 1.2:1. More than likely, it will be considerably below that value. Those times, when I do wind up with a 2:1 VSWR, it always turns out to be my fault for not reading the dial correctly. I have set the dial at 55 rather than 65, all of this without putting a signal on the air. When the time arrives that I have an amplifier in line, and up and running, it too will have a dial setting chart, compiled by operating the amplifier into a dummy load. If I can do this, so can you!!!

**LeRoy E. Smith, WB0LTV, Hot
Springs, South Dakota 57747**

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New
220 MHz

220: FM for All!



Kenwood brings you a wide range of 220 MHz gear designed for every need. Choose from two types of mobile and two types of HT. The TH-315A is a

TH-315A
Full-featured HT

full-featured HT covering 220–225 MHz. Ten memory channels and 2.5 watts of power. (5 W with PB-1 or 12 V DC.) Uses the same accessories as the TH-215A for 2 meters or TH-415A 440 MHz. For truly "pocket portability," choose the TH-31BT, a thumb-wheel programmable, 1 watt unit. For mobile use, select the TM-321A or TM-3530A.

The TM-321A is the 25 W, 220 MHz, 14-memory version of the super popular, super compact TM-221A. The 25-watt TM-3530A has 23 memories, a 15 telephone number memory and auto dialer. Direct keyboard frequency entry and front panel DTMF pad enhances operating convenience. Novice to Amateur Extra, these transceivers will put everyone on the air "Kenwood Style"!

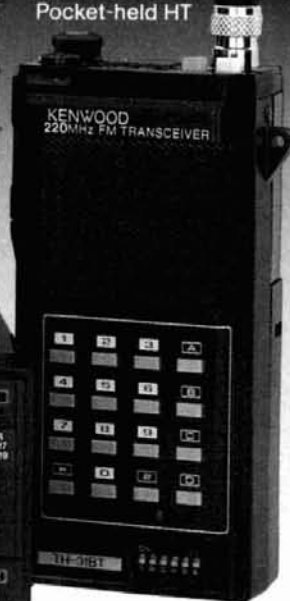
TM-321A
Compact mobile transceiver

TH-31BT/31A
Pocket-held HT

New



TH-315A



New

TM-3530A
Full-featured mobile transceiver

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The TM-321A comes with 16-key DTMF mic. A complete line of accessories is available for all models.

Complete service manuals are available for all Kenwood transceivers and most accessories. Specifications and prices are subject to change without notice or obligation.

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MFJ multi-mode data controller



9 modes for only . . . \$249.95

Amateur radio's most versatile multi-mode data controller -- the MFJ-1278 -- lets you join the fun on Packet, AMTOR, RTTY, ASCII, CW, Weather FAX, SSTV, Navtex and gives you a full featured Contest Memory Keyer mode . . . you get 9 modes . . . for an affordable \$249.95.

Plus you get MFJ's new **Easy Mail™** so you and your ham buddies can leave messages for each other 24 hours a day.

You'll find it the **most user friendly of all multi-modes**. It's menu driven for ease of use and command driven for speed.

A high resolution 20 LED tuning indicator lets you **tune in signals fast in any mode**. All you have to do is to center a single LED and you're **precisely tuned in to within 10 Hz** -- and it shows you which way to tune!

Plus you get 32K RAM, KISS for TCP/IP, high performance HF/VHF/CW modems, software selectable dual radio ports, AC power supply and more.

All you need to join the fun is an MFJ-1278, your rig and any computer with a serial port and terminal program.

You can use the MFJ Starter Pack to get on the air instantly. It includes computer interfacing cable, terminal software and friendly instructions . . . everything you need to get on the air fast. Order MFJ-1282 (disk)/MFJ-1283 (tape) for the C-64/128 and VIC-20; MFJ-1287 for Macintosh; MFJ-1284 for the IBM or compatible, \$19.95 each.

Packet

MFJ's new generation packet mode gives you genuine TAPR software and hardware plus many MFJ enhancements like Easy Mail™.

A new Kiss interface makes the MFJ-1278 TCP/IP compatible.

Extensive tests published in **Packet Radio Magazine** ("HF Modem Performance Comparisons") prove the TAPR designed modem in the MFJ-1278 gives better copy with proper DCD operation under all tested conditions than the other modems tested.

New AMTOR mode!

Now the MFJ-1278 has a new AMTOR and Navtex mode, making it the only controller to feature **nine** digital modes.

MFJ-1278 transmits and receives AMTOR and includes all AMTOR modes: ARQ (Mode A), FEC and MODE S (Mode B).

Baudot RTTY

You can copy all shifts and all standard speeds including 170, 425 and 800 Hz shifts and speeds from 45 to 300 baud. You can copy not only amateur RTTY but also press, weather and other exciting traffic.

You can transmit both narrow and wide

shifts. The wide shift is a standard 850 Hz shift with mark/space tones of 2125/2975 Hz. This lets you operate MARS and standard VHF FM RTTY.

ASCII

You can transmit and receive 7 bit ASCII using the same shifts and speeds as in the RTTY mode.

CW

You get a Super Morse Keyboard mode that lets you send and receive CW effortlessly, including all prosigns -- it's tailor-made for traffic handlers.

A huge type ahead buffer lets you send smooth CW even if you "hunt and peck".

You could store entire QSOs in the message memories, if you wanted to! You can link and repeat any messages for automatic CQs and beaconing. Memories also work in RTTY and ASCII modes.

A **tone Modulated CW mode turns your VHF FM rig into a CW transceiver** for a new fun mode. It's perfect for transmitting code practice over VHF FM.

An AFSK CW mode lets you ID in CW.

You also get a random code generator that'll help you copy CW faster.

Weather FAX

You'll be fascinated as you watch WEFAX signals blossom into full fledged weather maps on your Epson or IBM graphics compatible printer.

Automatic sync and stop lets you set it and leave it for no hassle printing.

You can save FAX pictures and WEFAX maps to disk if your terminal program lets you save ASCII files to disk.

Pictures and maps can be saved to disk or printed to screen in real time or from disk if you have an IBM or Macintosh with the MFJ Starter Pack.

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A SIMPLE DIRECT CONVERSION TRANSCEIVER

By Rodney A. Kreuter, WA3ENK, 319 McBath Street, State College, Pennsylvania 16801

Here's another project using the NE602

I've always wanted to build a direct conversion receiver, but parts availability was a problem. I needed balanced mixers, matched schottky diodes, a good oscillator, and trifilar transformers. Then I received a sample of the Signetics NE602 and the incentive to build my receiver.

Of course, once you've built a direct conversion receiver, it's a simple matter to add a transmitter. And a keyer. And a good audio filter. And a digital readout. And a wind powered, nuclear backed-up power plant. And . . . And I wonder why I never get around to so many projects.

NE602

The NE602 is a relatively simple chip. I guess that's why I like it. Contained inside an eight-pin dip is a double-balanced mixer with about 15 db of gain, an oscillator, and a voltage regulator.

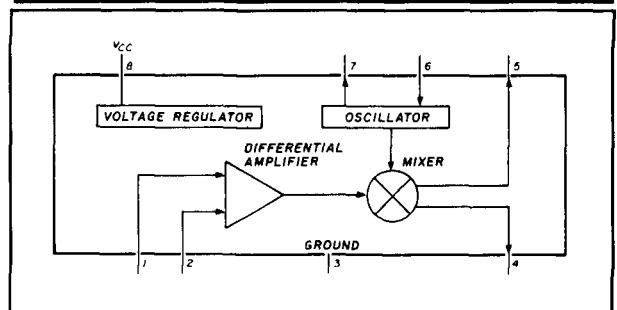
The chip was intended for the cellular radio market. The oscillator is good to 200 MHz and the mixer to 500 MHz. Not bad for less than 3 mA at 6 volts. (One of the Signetics application notes mentions that some people have used the mixer to 900 MHz, but they only guarantee it to 500 MHz.) It runs on 4.5 to 8 volts. But please, decouple the supply to the 602 with at least a resistor and a good bypass capacitor.

Inside the NE602

For a look inside the NE602, refer to **fig. 1**.

Input to the double-balanced mixer is differential (pins 1 and 2). If you don't have a differential signal, feed the signal into either input and bypass the other to ground

FIGURE 1



Basic functional block diagram of NE602.

with a capacitor. Under *no* circumstance should you provide a DC path from either input to ground. A DC path between inputs is okay. Input resistance is about 1.5k and input capacitance is about 3 pF.

The oscillator is very simple. It's a transistor connected as an emitter follower with an internal resistor of 20k from the emitter to ground. If you want to try to push the upper frequency limit, connect an external resistor (22k minimum) from pin 7 (the emitter) to ground. This will increase the current and raise the Ft of the transistor. The base of the transistor is available at pin 6. It's already DC biased so don't provide a DC path from pin 6 to Vcc or ground. The output of the oscillator is internally connected to the other input of the double-balanced mixer.

The mixer output is also differential (pins 4 and 5) and has an output impedance of 1.5k. If you don't want a differential output, use one output and leave the other disconnected. Remember, this mixer has about 15 db of gain. One bad point — you can't push much of a signal through this mixer. It's third-order intercept is about -15 dBm. This is quite normal for a receiver, but it wouldn't make a great mixer for a transmitter power chain unless you mixed at a low level and provided a lot of gain after it.

The voltage regulator isn't mentioned much in the

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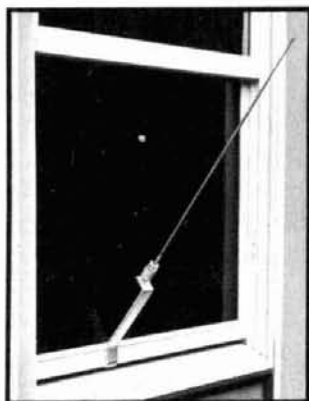
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Signetics literature. My measurements and some data sheet "reading between the lines" lead me to believe it's about 4 volts. The *absolute* maximum input voltage to the regulator is 9 volts; maximum recommended input is 8 volts. It might be nice to use a 12-volt supply but you'll have to knock it down with a Zener or another regulator first.

Basic specifications for the NE602 are:

Power supply	4.5 to 8 volts	
Current consumption	2.4 mA	(typical)
Maximum mixer frequency	500 MHz	(typical)
Maximum oscillator frequency	200 MHz	(typical)
Noise figure	5 dB	(at 45 MHz)
Mixer gain	15 dB	(at 45 MHz)
Third-order intercept	-17 dBm	(maximum)
Mixer input resistance	1.5k	(typical)
Mixer input capacitance	3pF	(typical)
Mixer output resistance	1.5k	(typical)
Mixer input capacitance	3 pF	(typical)
Mixer output resistance	1.5k	(typical)

Direct conversion receiver basics

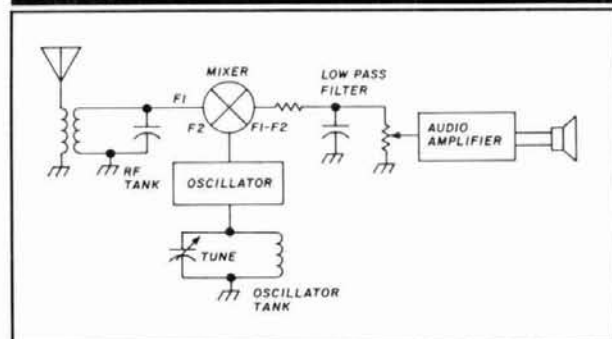
Direct conversion receivers have been sort of a fad for the past few years. If you need a refresher on the basics refer to **fig. 2**.

The RF signal is coupled into the mixer by the RF tank. The oscillator tank determines the oscillator frequency. The mixer combines these two frequencies and produces (at the output) the sum and difference of the two frequencies, plus the two original frequencies (at a minimum). If the oscillator frequency is very near the RF frequency, one of the output frequencies (the difference) will be in the audio range. The other frequency (the sum) will be at RF and will be attenuated by the low-pass filter. The remainder of the receiver is provided by lots of audio gain.

Most direct conversion receivers suffer from two problems:

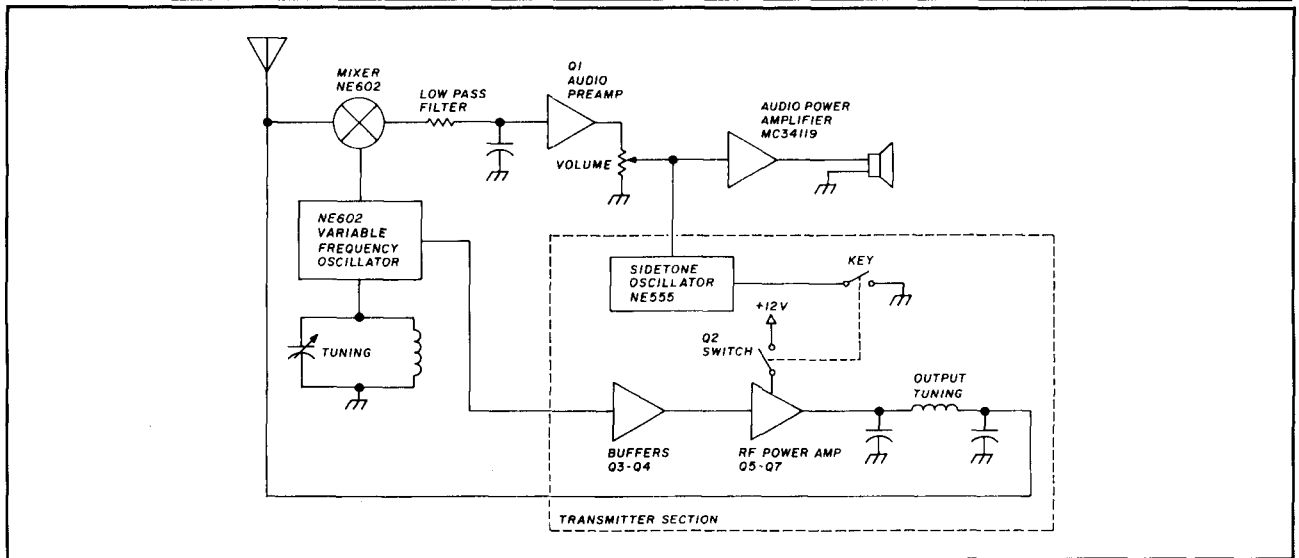
- Microphonics — Because most (if not all) of the signal gain is at an audio frequency, any slight vibration which might change

FIGURE 2



Block diagram of a typical direct-conversion receiver.

FIGURE 3



Block diagram of the direct-conversion transceiver.

the local oscillator comes through the speaker.

AC Hum — A 60-cycle hum created when operated from an AC supply.

These aren't real difficulties with the NE602. Using the NE602 won't cure the problems completely, but it will reduce them by two orders of magnitude. Most direct conversion receivers use diodes for a mixer. Instead of gain, these actually have about 6 dB of loss. The mixer used in the NE602 has about 15 dB of gain. Therefore the signal coming out of the mixer is about 20 dB higher in amplitude than one from a diode mixer. This means that a lot less audio gain is required after the mixer, and fewer audio problems occur.

Circuit description Receiver

The receiver is very straightforward. (See figs. 3 and 4.) L2, C1 and C2 provide a broadband balanced input to the double-balanced mixer of the NE602. C13 through C18, and L3 are the tank and feedback circuits for the oscillator section of the chip. I realize you might question using six capacitors for an oscillator, so let me explain.

Capacitors C13 and C14 provide the feedback voltage divider for the oscillator. Capacitor C15 prevents the inductor from upsetting the DC bias of the oscillator. Capacitors C16, C17, and C18 are somewhat tricky.

These days it's very hard to get a good, affordable air-variable capacitor. I decided to use three capacitors instead. You'll find that by playing with these three capacitors, you can adjust the tuning range to almost anything you want. My prototype tunes from about 6.9 MHz to about 7.4 MHz, using the values shown. (Watch out

for those band edges!) Decreasing C17 will make the tuning range smaller. If you have a 100-pF air variable, you may want to decrease C17 in order to make tuning a little easier. You can use a smaller "fine-tuning" capacitor in parallel with C18 with good results. A vernier dial might also come in handy here. Remember that this oscillator is also your transmitter VFO. Stability is everything!

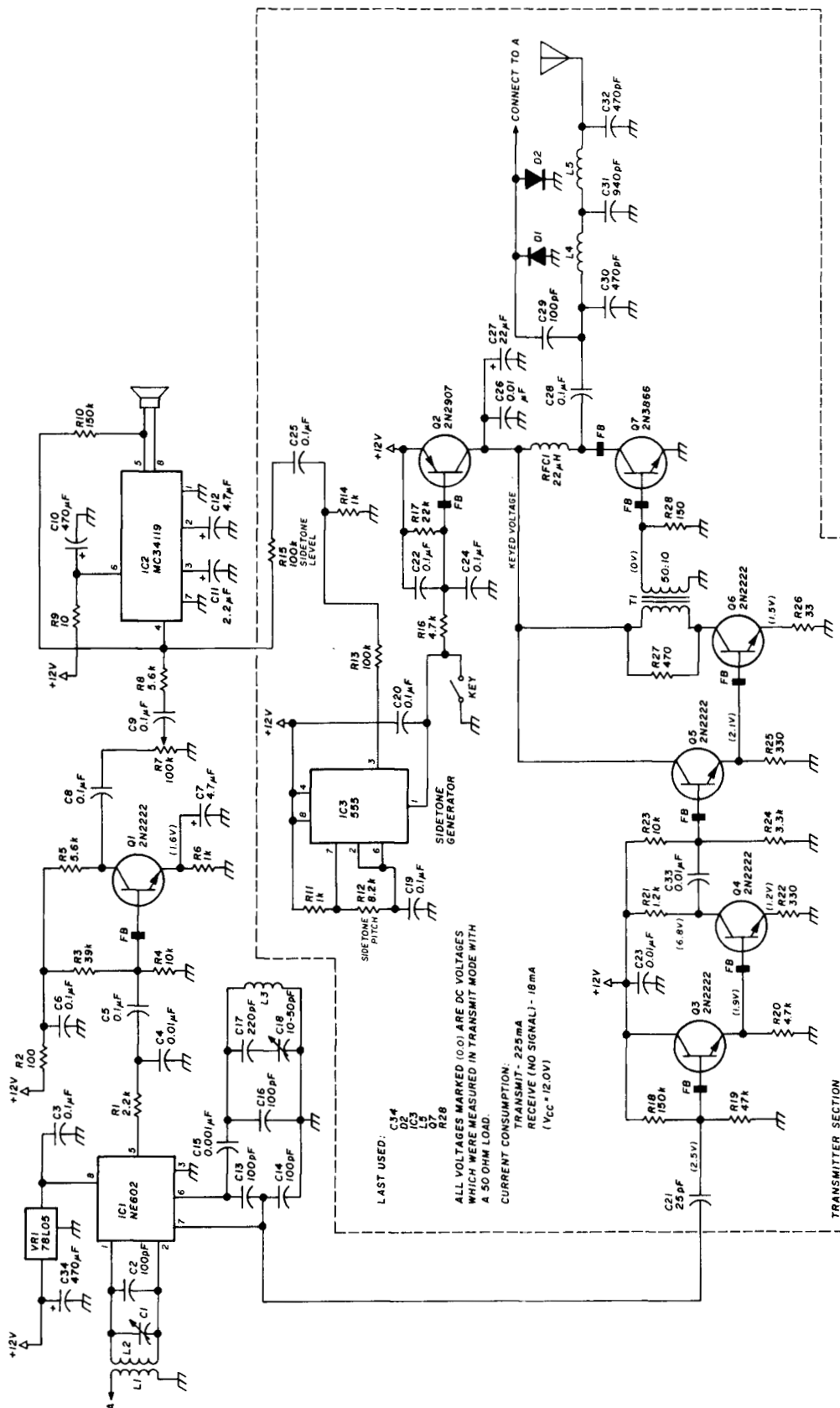
Since I've already mentioned that the NE602 contains a voltage regulator, you're probably wondering why I used a 78L05 to regulate the voltage to the NE602. First, it never hurts to have a good stiff power supply for an oscillator. Second, it's used to isolate the NE602 from the power supply. My first prototype (there were four) simply used a resistor and a capacitor for power supply decoupling. I had a lot of audio gain and the feedback was terrible. The 78L05 isolates the NE602 very well.

R1 and C4 are used as a low-pass filter for audio (about 4.3 kHz including the 1.5k output impedance of the NE602). R2 and C6 are used to prevent the audio output from reaching Q1 through the power supply.

Q1 is a simple audio-gain stage. I originally used a dual op amp for this function, but found that I didn't need nearly that much gain. The gain of Q1 in this configuration is about 150-200. Resistor R3, one of the bias resistors, can be varied to adjust the gain if you feel it's necessary. Lowering R3 will increase the gain. Just be sure not to saturate Q1.

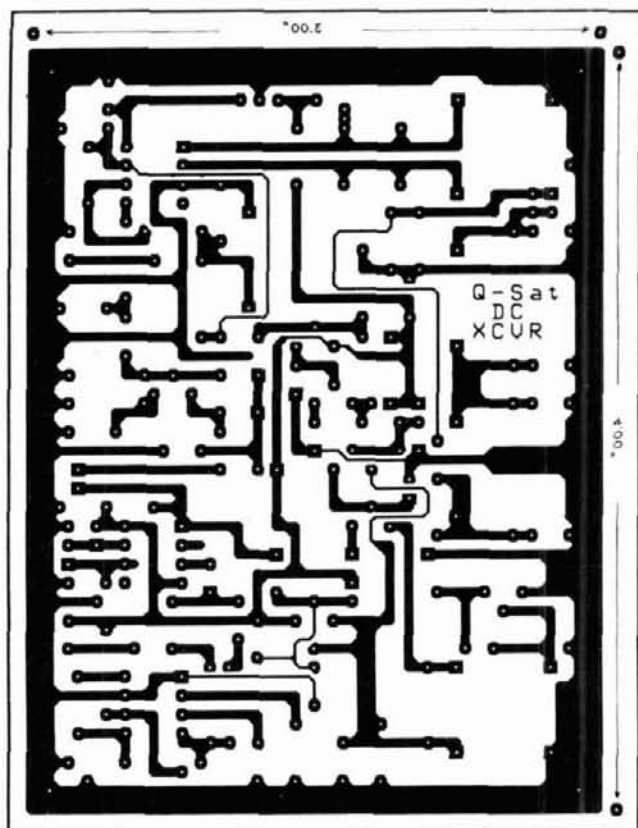
IC2 is an audio power amplifier that seems to be replacing the LM386. The output is differential and doesn't require a large capacitor to couple it to the speaker. Just keep the speaker leads short (a few inches) and twist them tightly. R9 and C10 decouple the amplifier from the power supply and are necessary to prevent

FIGURE 4



Schematic diagram of a simple direct-conversion CW transceiver.

FIGURE 5



Printed circuit board layout.

audio feedback. After all, 80 dB of gain at one frequency is a little hard to control.

Transmitter

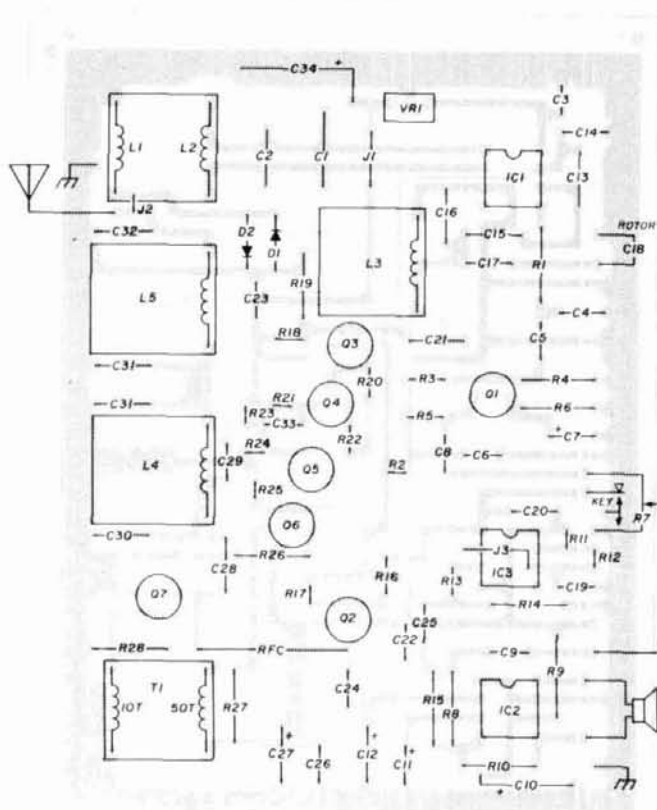
For the transmitter description refer to **figs. 3 and 4**. The oscillator output is coupled to an emitter follower (Q3) by means of C21. This provides buffering of the oscillator so that the transmitter doesn't "pull" it.

Transistor Q4 provides the first voltage gain for the RF signal. Its purpose is to supply enough drive for the next emitter follower, Q5. Most simple crystal-controlled transmitters probably wouldn't need this additional gain because their oscillators provide enough output power to drive a 1-watt output stage directly.

Q5 provides a low impedance drive for the input of the first class "C" amplifier, Q6. Transformer T1 is used mainly to furnish a high impedance load for Q6 and a low impedance drive for Q7. I tried to do away with T1 by using another emitter follower in its place. It worked, but not very well. The two transistors consumed too much power. This was unacceptable because this transceiver was designed to be battery operated.

Q7 is used as the RF power amplifier. A 2N3866 or a

FIGURE 6



Parts placement.

2N3553 seemed to work well. Notice the double pi output filter. I used a double pi filter instead of the more common single pi to ensure a clean output. I would have liked to use variable capacitors for C30, C31, and C32, but I wanted to keep the circuit as simple as possible and I knew that good variables for these capacitors can be hard to obtain. It may be difficult to find a 940-pF capacitor for C31. The pc board is laid out to accept two capacitors in this position. Use any parallel combination to get 940 pF.

IC3 is a 555 used as a side-tone monitor. You can adjust the pitch of the side tone by changing R12. A lower value increases the pitch. Adjust side-tone volume by changing R15.

Capacitor C29 couples energy from the antenna into L1 for the receiver. Diodes D1 and D2 protect the front end of the receiver during transmit. If you're going to build just the receiver, place a jumper (J2) on the board to couple the antenna into L1. You won't use the double pi network unless you're also building the transmitter section. Omit J2 if you're building the complete transceiver.

Transistor Q2 keys the power to transistors Q5, Q6,

PARTS LIST

Receiver	
* C1	50 or 60 pF trimmer
C2, C14, C16, C13	100 pF
C3, C5, C6, C8, C9	0.1 μ F
C4	0.01 μ F
C7, C12	4.7 μ F 16 volt
C10, C34	470 μ F 16 volt
C11	2.2 μ F 16 volt
C15	0.001 μ F
C17	100 to 220 pF (see text)
* C18	10-50 pF variable (see text)
* IC1	Signetics NE602 (Oscillator/mixer)
* IC2	Motorola MC34119 (Audio power amp)
L1	30 turns no. 26 on T-37-2 core
L2	5 turns no. 26 over L1
L3	25 turns no. 26 on T-37-2 core
* Q1	2N2222
R1	2.2k
R2	100 ohms
R3	39k
R4	10k
R5, R8	5.6k
R6	1k
R7	100k audio taper
R9	10 ohms
R10	150k
* VR1	78L05 (5-volt voltage regulator)
* Printed Circuit Board	
* (2) T37-2 Toroid cores	
* (1) Ferrite bead	
Transmitter	
C19, C20, C22	0.1 μ F
C24, C25	0.1 μ F 50-volt minimum
C28	0.1 μ F 50-volt minimum
C21	25 pF
C23, C26, C33	0.01 μ F
C27	22 μ F 16 volts
C29	100 pF
C30, C32	470 pF
C31	940 pF (or two 470 pF in parallel)
* D1, D2	1N914 or 1N4148
* IC3	NE555 (Side-tone oscillator)
L4	15 turns no. 26 on T-37-2 core
L5	15 turns no. 26 on T-37-2 core
* Q2	2N2907
* Q3, Q4, Q5, Q6	2N2222
* Q7	2N3866 or 2N3553
R11, R14	1k
R12	8.2k
R13, R15	100k
R16	4.7k
R17	22k
R18	150k
R19	47k
R20	4.7k
R21	1.2k
R22, R25	330 ohms
R23	10k
R24	3.3k
R26	33 ohms
R27	470 ohms
R28	150 ohms
* RFC1	22 μ H
T1	Primary 50 turns no. 30 enamel Secondary 10 turns no. 26 on T-37-2 core
* (3) T-37-2 Toroid cores	
* (6) Ferrite beads	

The following may be ordered from:

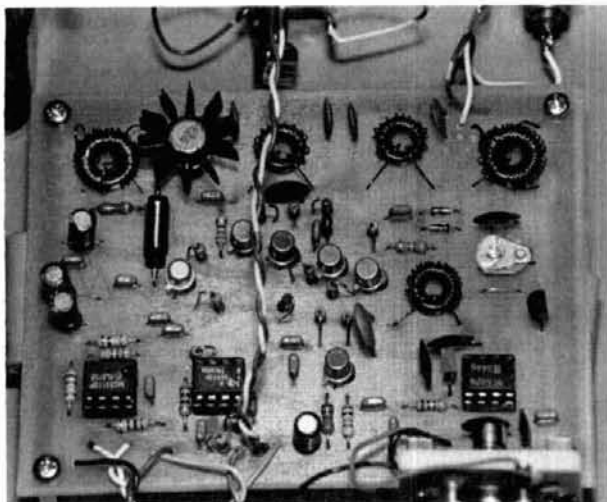
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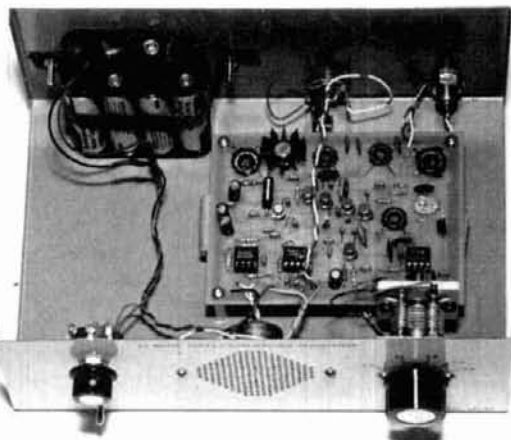
and Q7. Resistor R16 and capacitor C24 provide output wave shaping. You may increase capacitor C24 to provide a "softer" output waveform.

PHOTO A



Top view of pc board. The two 470- μ F caps are mounted underneath.

PHOTO B



Inside View. There's still plenty of room for an audio filter.

Construction

I recommend using the pc layout in **figs. 5 and 6**. There's a lot of gain in this receiver and the transmitter has enough of its own.

Fifteen turns of wire on a toroid core sounds simple enough, but don't believe you can't tweak a toroid coil. Spreading out or compressing the turns can change the inductance about 10 percent. If you have a grid-dip meter, you must couple into a toroid with a single-turn link. Don't expect to make any reasonable measurements just by placing the dip meter near a toroid. Remember that turns on a toroid are counted by the number of turns on the inside of the core, not the outside.

Mount the variable capacitor (C18) firmly. Hand



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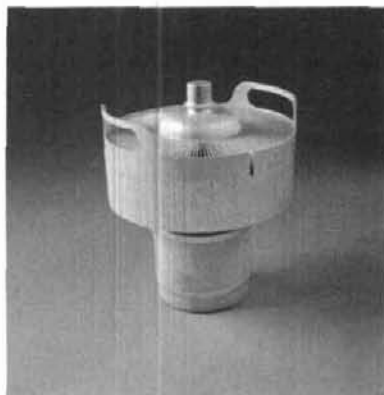
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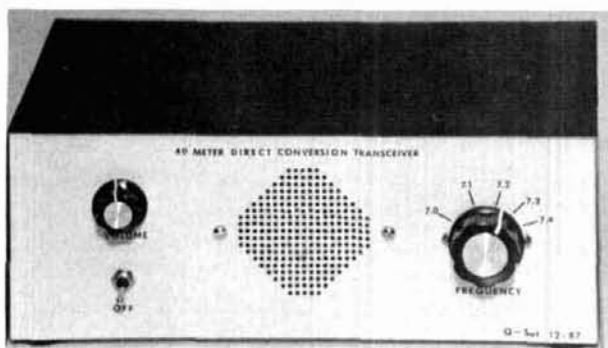
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PHOTO C



The completed unit. Antenna and key connectors are on the rear panel.

capacitance can be a problem before it's put in a metal case. Also make sure that the rotor is the terminal used for ground. See photos A and B for internal details. Photo C shows the completed unit.

Don't expect reasonable performance without a reasonable antenna. Although I've been known to throw a piece of wire on the family room floor and attempt to listen to the receiver, it doesn't work very well. A good ground helps.

I mounted some resistors in a vertical position on the pc board to save room. In these cases, one of the pads will be square. Mount the body side of the resistor to the square pad.

Modifications

You can make the basic transceiver work on almost any band; however, operation above 20 meters might be difficult due to the stability of the oscillator.

An audio filter would make a nice addition. It should be easy to add one in series with the volume control, because wires are brought out from the board at this point.

Stability

Before I address the topic of stability, I'd like to recommend that you don't attempt to build any transmitter if you don't have a scope (or better yet, a spectrum analyzer) or access to one. Tracking down stability problems without one is simply too frustrating. A local ham club certainly should be able to help. I know that many people will think that a properly designed transmitter should be no problem, and if we all used 50-ohm load resistors instead of antennas, that would be true. The difficulty is that it's impossible to design an efficient transmitter that will work with any given load.

My basic philosophy about stability is that I would rather put a clean 1/2-watt signal into an antenna than a dirty 10-watt one. Even if the "spurs" are 30 dB down,

I'm not satisfied. Spurs should be down a minimum of 50 dB.

I did have some stability problems. When I fired up the transmitter, it was into a very good 50-ohm load. The output was about 3/4 watt (17 volts p-p), and it was very clean across the entire tuning range. Then came the antenna test — or rather the antenna disaster. I'll be the first to admit that this antenna leaves a lot to be desired. I've moved recently, and haven't had time to do a proper job of planting the antenna farm. The antenna in question is a simple half-wave dipole about 10 feet off the ground at one end and 20 feet at the other. It resonates somewhere. Anyway, the output was fine at some frequencies. At others there was some 7 MHz energy left, but not much.

The solution wasn't simple. First of all, it seemed that transformer T1 was ringing like mad. Lowering the value of resistor R28 and adding R27 calmed it down. The input of the output transistor (2N3866) I used looks very capacitive at 7 MHz. R28 prevents this capacitance from resonating with the secondary of T1. This cleaned up 90 percent of the problem. Next I "empirically derived" (played with) the turns ratio of T1. This helped a little. I reduced the "Q" of T1 using R27; this helped a little more.

I also found out that I didn't have enough drive, so I went back to the proverbial drawing board and added stage Q4. One tip — if you're not getting at least 600 to 800 mV p-p at the emitter of Q3, play with the ratios of C13 and C14. I tried making C13 as small as possible, but I didn't get enough drive for Q3 until I increased C13 to 100 pF.

Stubborn cases may require a resistor in parallel with RFC1; a thousand ohms should do it. And don't forget

TABLE 1

The following voltages (p-p and DC) are given as an aid in troubleshooting any problems you might have. All of the signals are 7-MHz sine waves. Data was taken with a 12-volt power supply and the unit was in the transmit mode with a 50-ohm load.

	AC (p-p)	DC
Emitter of Q3	700 mV	1.9 volts
Collector of Q4	1.1 volts	6.8 volts
Emitter of Q5	1.6 volts	2.1 volts
Collector of Q6	17 volts	12 volts
Base of Q7	2.9 volts	0 volts
Collector of Q7	18 volts	12 volts
Antenna Output (50-ohm load)	18 volts	0 volts
NE602 (pin 7)	700 mV	4.5 volts

the ferrite beads on the collector and base of Q7 and the other transistors.

Table 1 gives typical voltages for troubleshooting purposes.

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Article A

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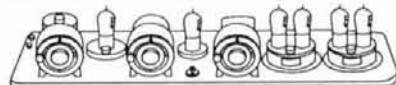


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THE WEEKENDER



Build this simple L-C checker

This simple capacitance-inductance checker measures capacitance to approximately 1000 pF and inductance to 50 μ H. I first saw it described in *QST* some 36 years ago.¹ That version used a filament-type tube (3A5) in a self-rectifying oscillator powered from 115 volts AC. I built one in a cigar box lined with metal foil. It's seen constant use in my shack with the original tube!

The initial L-C checker measured capacitance only. I modified it to add inductance measuring capability when I transistorized the unit.

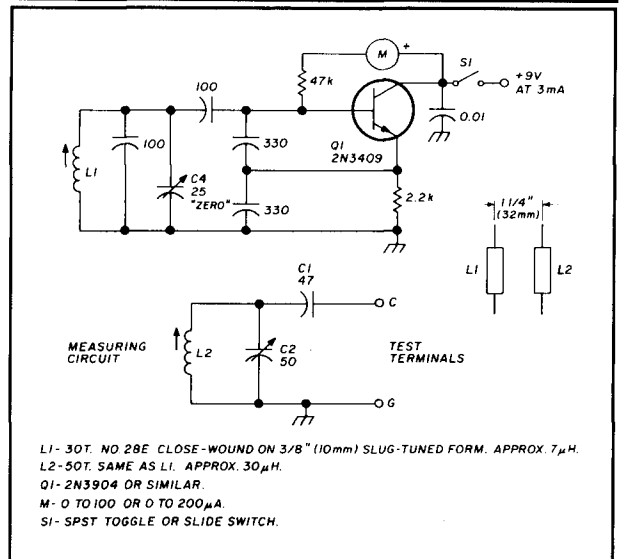
The capacitance circuit measures to 5000 pF or more; however, accuracy and resolution are reduced above 1000 pF because of circuit limitations. But, when you pick a mica capacitor marked with two red dots from your junkbox, this unit will quickly tell you if it's 2.2, 22, or 220 pF. The device has the advantage of applying no voltage or current (other than a few millivolts of RF) to the capacitance or inductance under test.

How it works

The circuit is based on the "grid-dip" or absorption effect, which occurs when a parallel resonant circuit is coupled to an oscillator of the same frequency. If you look at **fig. 1**, you'll see that Q1 operates in a conventional Colpitts oscillator circuit at a fixed frequency of approximately 4 MHz. The exact frequency isn't critical. A meter connected in series with the transistor's

By Jack Najork, W5FG, 723 Flamingo Way, Duncanville, Texas 75116

FIGURE 1



Schematic diagram of L-C checker with measuring circuit for measurement of capacitance only. L1 and L2 should be spaced as shown for optimum electrical coupling.

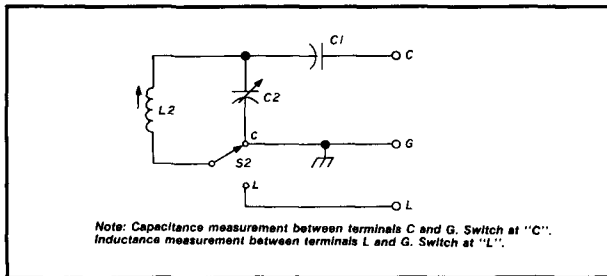
base-bias resistor serves as the "dip" or absorption indicator.

The variable measuring circuit consists of C1, C2, and L2 and is connected to panel terminals as shown. L2 is loosely coupled to L1 in the oscillator circuit. This measuring circuit is tuned to the oscillator frequency with variable capacitor C2 set at full or (maximum) capacitance. When power is applied to the oscillator the meter shows a dip caused by power absorption by the measuring circuit.

Connecting an unknown capacitor across the test terminals lowers the resonant frequency of the measuring circuit. To restore resonance, tune capacitor C2 lower in capacitance. The meter will dip again when you reach this point. Determine the capacitance across the test terminals by calibrating the dial settings of C2. More on this later.

Capacitor C4, a small variable trimmer in the oscillator circuit, compensates for drift or other variations and is normally set at half capacitance. It's a panel control, labeled "ZERO", and is used to set the oscillator exactly at the dip point when C2 is set at maximum capacitance. This corresponds to zero on the calibration scale.

You can also use C4 to compensate for the capacitance inherent in long leads running from the test terminals to the unknown capacitor. The leads are connected to the test terminals and dressed close to the capacitance to be measured, but not connected to it. Adjust C4 for a dip with C2 at zero. Then connect the leads and make your measurement.

FIGURE 2

Addition of S2 to the measuring circuit enables measurement of both capacitance and inductance. Note: For capacitance measurement between terminals C and G, switch at "C". For inductance measurement between terminals L and G, switch at "L".

Measuring inductance

After I got the transistorized version working, it occurred to me that I should be able to use the circuit to measure inductance as well. **Figure 2** shows how. The oscillator circuit remains unchanged. Add an SPDT switch (S2) to the measuring circuit. With S2 in the "C", or capacitance measuring position, the circuit is as before. In the "L", or inductance measuring position, the switch disconnects the bottom of L2 from ground and connects it to a third panel terminal marked "L".

Connecting an unknown inductance across the "L" and "G" terminals again lowers the resonant frequency of the measuring circuit because the unknown inductance is now in series with L2. You must tune C2 lower in capacitance again to restore resonance. As with capacitance measurements, the best resolution occurs at the lower inductance values.

To measure inductance, set S2 to "C" and adjust the oscillator (ZERO) control for a dip with C2 at zero. Set the switch to "L" and connect the unknown inductance across the "L" and "G" terminals.

Construction notes

You'll need solid construction for consistent calibration accuracy. Use the VFO construction techniques from any handbook. Choose a good-sized, sturdy metal cabinet so that you can use a large dial or pointer for the measuring capacitor, C2. I glued a 2-inch pointer to my dial and spread the calibration marks across the largest dimension of the cigar box.

The spacing (electrical coupling) between L1 and L2 isn't critical, though it can be adjusted if necessary. Wider spacing produces a shallower dip, but improves the measuring resolution. Conversely, closer spacing (coupling) produces a more pronounced dip, which lowers resolution.

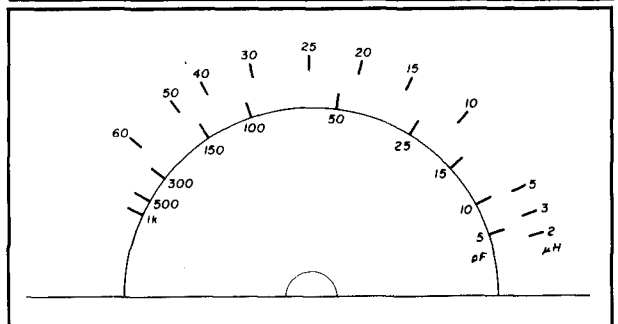
Make the wiring from the bottom of L2 to switch

S2, and from S2 to the panel terminal "L", short and low inductance. Use heavy wire or copper ribbon, because these connections form a portion of the unknown inductance placed across terminals "L" and "G". Too much inductance in these connections produces erroneous inductance readings when measuring very small inductances.

Calibration

Calibrate the capacitance range by placing known values of capacitance across the "C" and "G" terminals and marking these values on the C2 dial or pointer. Most of us have enough well-marked mica and ceramic capacitors in our junkbox to make this easy. Don't forget, you can also use these capacitors in parallel or series, as needed.

Inductance scale calibration is a bit tougher. You might want to beg, borrow, or otherwise obtain a collection of small, molded RF chokes. I had a half dozen 10- μ H chokes and used them in series and parallel to calibrate. This method may not result in laboratory-type accuracy, but it'll bring you right into the ballpark. **Figure 3** shows my unit's calibration.

FIGURE 3

Typical range scale calibration made with C2 and 50 pF, Hammarlund HF 50 with semi-circular plates. Capacitors with a different plate shape will yield a different calibration.

Using other parts

You engineering types will by now have observed that juggling the values of C1 and C2 alters the range and linearity of the measuring range. For example, increasing C1 expands the calibration at the low picofarad end but limits the upper capacitance measurement. If L2 is an adjustable coil, as shown, select C1 and C2 for the desired results, retuning L2 as needed to restore resonance.

If your junkbox dictates, use a larger value capacitor for C2. This requires increasing the value of C1. One possible combination is 150 pF for C2 and 130 pF for C1, with L2 reduced to approximately 10 μ H. To limit the inductance measuring range with this com-

bination it's necessary to add a small fixed capacitor in parallel with C2. Try 10 to 15 pF.

If the required microammeter isn't available, take heart. Since the unit draws around 3 mA at 9 volts, you can use a zero to 5 mA meter in series with the + lead to the power source. Resonance will now be indicated by a *rise* in the meter reading instead of a dip. The variation between dip and non-dip won't be as pronounced as with a base current meter, but it will be usable.

If 3/8-inch diameter coils aren't available you can use 1/4-inch forms. Scrounge them from the i-f section of a defunct TV set. You'll need more turns, and the "Q" will be a bit lower, but they'll work. Conversely, for those who want improved resolution, substituting larger diameter coils wound with heavier wire will increase "Q". This enables looser coupling which in turn produces a sharper dip.

References

1. *QST*, March 1952.
Article B

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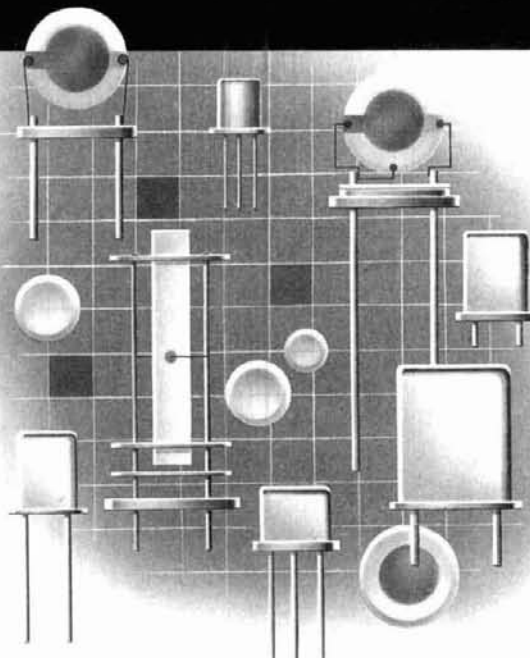
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HAM RADIO TECHNIQUES

Bill Orr, W6SAI



New Zealand, Maui, and the Solar Cycle

My visit to New Zealand was wonderful! I attended and spoke at the NZART (New Zealand Association of Radio Transmitters) Convention at Whakatane. Then I took a leisurely trip around the North Island, visiting such notables as ZL1AAS, ZL1BRQ, ZL1SZ, ZL2JQ, and ZL2AM. The combination of hospitality and beautiful countryside was overwhelming. I had the privilege of operating with my reciprocal call, ZLØSAI. It's interesting to hear what a pile-up on 20-meter SSB sounds like from the DX end. After a quick call, the S meter on the KWM-2 went over against the pin and stayed there! Beaming north-east across the United States and into Europe, it was interesting to note that the European signals were almost as loud as the W6s. Ear-splitting signals were also noted from "locals" like UJ8, UD6, 9N1, and 4S7.

I saw more homemade tilt-over towers in New Zealand than I'd ever seen in California. The crank-up tower doesn't seem to be very popular; many DXers favor the tilt-over type. Most of them use a 20-foot high base structure and a tilt-over top section, ranging from 18 to 25 feet long. Some monster tilt-over towers, like the one at ZL1AAS, are nearly 80 feet high. All of them are counterbalanced so that

little effort is required to raise or lower the top section.

Do any of you have a homemade tilt-over tower? If so, I'd like to hear about it; send pictures and drawings, if possible.

The mild climate, beautiful scenery, and friendly people make New Zealand a perfect place to visit. On your way there, stop in Tahiti or Fiji for a touch of the exotic. Truly, New Zealand is a little corner of paradise! Thanks to all who made the visit so pleasant for me.

Next stop Maui

After New Zealand, I stopped at Maui, Hawaii and visited Steve, KH6SB, who runs the island's NOAA Ionospheric Observatory. Here, talk turned to DX and the sunspot cycle. Steve showed me readings and graphs taken from recent ionospheric sounding measurements. I remembered various statements in DX newsletters predicting that the peak of cycle 22 might be greater than any previously experienced, and that it could be reached as soon as December 1988 — right about now. I queried Steve about this. His data indicated that the International Smoothed Sunspot Number (taken as gospel by many Amateurs) showed a cycle quite different from the Geomagnetic A Index, the Ottawa Radio Flux (10 cm), or the ionospheric measurements of the maximum frequency of F_2 reflection measured at

Maui. (See fig. 1.) According to Steve, a lot depends upon which cycle you're talking about.

The Maui vertical sounding of the F_2 layer showed a minimum value centered about April/May, 1986. The smoothed sunspot numbers indicated a minimum falling during September 1986 for old cycle 21. The Geomagnetic Index indicated a minimum near January 1987, and the Ottawa Radio Flux had a broad minimum covering April 1985 to October 1986.

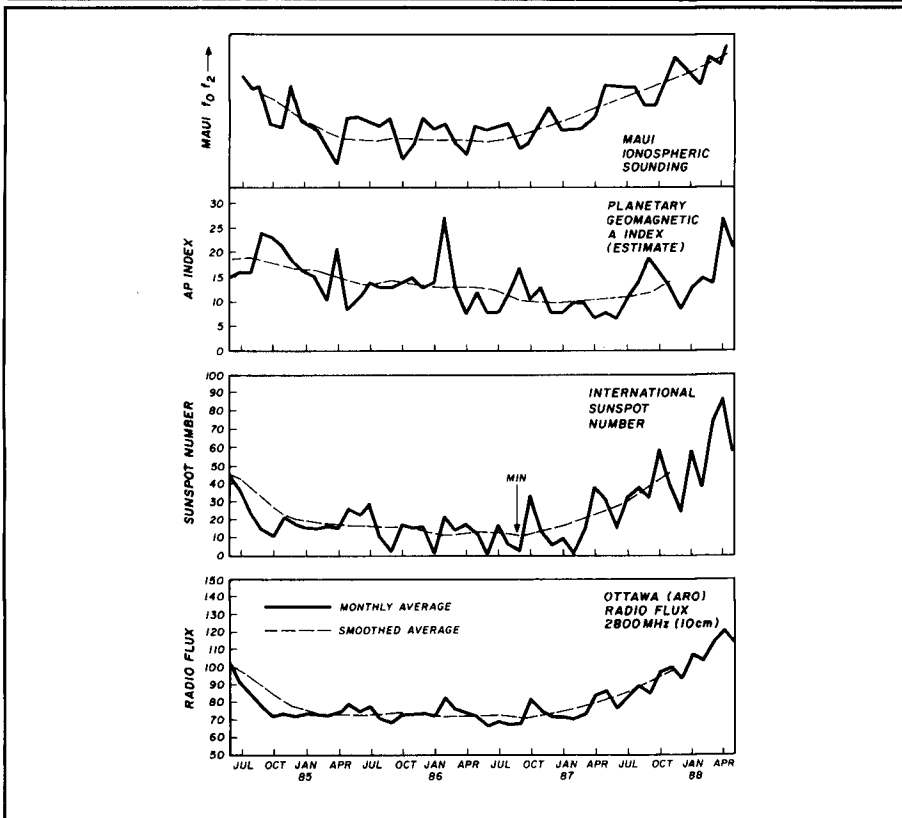
So where do we go from here? When will the present ionospheric cycle peak out? QST's "How's DX" column indicates a peak at the end of 1988. Steve showed me a graph of the median values of the maximum reflecting frequency of the F_2 layer, as measured at his station (fig. 2). He pointed out that the slope of the present increase is just about the same as that of the last cycle. Steve thinks that the peak of the present cycle may arrive around the fall of 1990, and that it will be very similar to the last.

Time will tell. Meanwhile, enjoy 10-meter DX and don't overlook the amazing things that are happening on the 6 and 2-meter bands.

RFI from cordless phones?

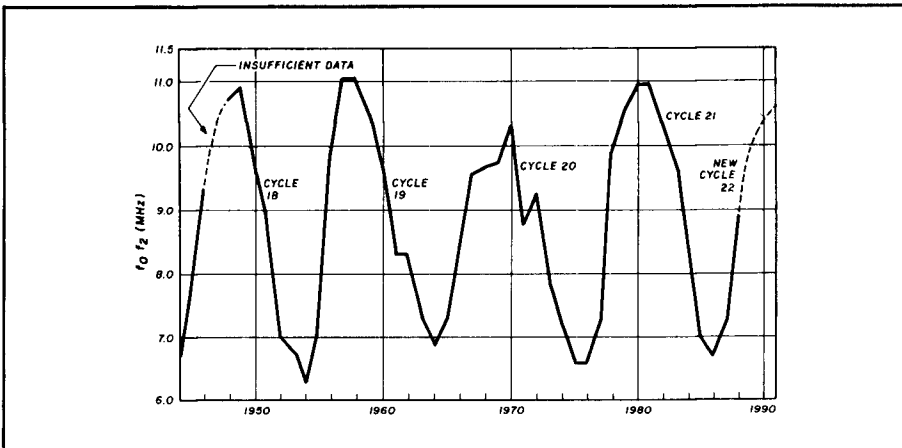
The June issue of *Modern Electronics* has an article by C. Hall describing TVI from a neighbor's cordless telephone. The phone transmitted

FIGURE 1



Comparison of cycles of ionospheric sounder (Maui) with A-index, sunspot number, and radio flux over the period July 1985 to April 1988 shows that the individual cycles have quite different minimums.

FIGURE 2



Median values for the month of May for the ionospheric readings at Maui, Hawaii in terms of maximum vertical reflected frequency (f_oF_2) of the F_2 layer. Note that the rising slope of cycle 21 and cycle 22 is approximately the same. The best estimate is that the present cycle will peak out in the fall of 1990.

FM signals on a frequency in the range of 46.61 to 46.97 MHz (base) and 49.67 to 49.99 (handset). These frequencies were perilously close to various TV pic-

ture i-f amplifier circuits that operate at 45.75 MHz.

A high-pass filter on the TV set did not do good; the cutoff frequency of the

filter was higher than the telephone band. The solution was to cut a linear trap made from 300-ohm ribbon line and place it across the receiver antenna terminals in parallel with the existing transmission line (fig. 3). The trap was cut to a length of 50.25 inches to tune it to the center of the cordless phone band. (This length takes into account the velocity of the propagation factor of the line.) Hall said this eliminated the herringbone lines on the TV screen caused by the cordless telephone.

A compact wire antenna for 7 and 21 MHz

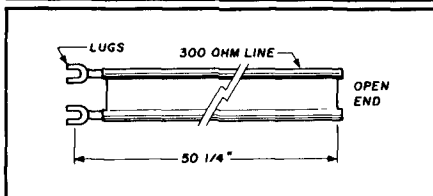
It's hard to be loud on a city lot, and erecting a 66-foot long, 40-meter dipole can be a challenge in some locations. Figure 4 shows a compact, space-saving antenna designed by V.C. Lear, G3TKN. It's been discussed in RSGB's *Radio Communication* and other European magazines. As far as I know, it hasn't been publicized on this side of the pond. In brief, it's a 40-meter dipole shortened to about 54 feet by folding the center portion of the radiator up into a two-wire transmission line. The lengths of the top section are chosen to provide two 5/8-wavelength sections in phase on 21 MHz.

The antenna supplies the usual figure eight pattern on 40 meters, and a somewhat narrower figure eight on 21 MHz. Best of all, there's about a 3-dB gain over an equivalent dipole on 21 MHz.

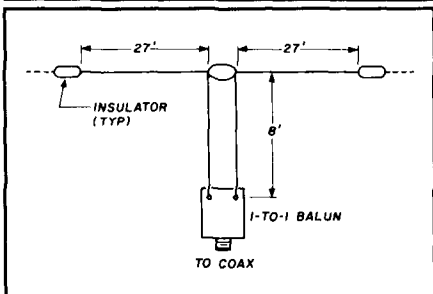
The folded, two-wire stub has a spacing of 6 inches and is made of no. 16 wire. The end of the stub is matched to a coax line by way of a 1:1 balun, like the Bencher ZA-1A.

The two-wire line is spaced with 3/8-inch diameter spreaders cut from Lucite®, Plexiglas®, or other insulating rod material. Holes are drilled at the outer ends to pass the wires, which are held in position by twisting short pieces of no. 22 wire around the spreader and the antenna wire. The spreaders are spaced about 18 inches.

An easy way to make the line is to stretch two 10-foot lengths of wire

FIGURE 3

High-pass filter designed to attenuate TV interference from cordless telephones operating in 49 to 50 MHz region.

FIGURE 4

Compact 7/21 MHz antenna attributed to G3TKN. The 8-foot stub is made of no. 22 enamel coated wire, spaced 6 inches.

under tension between two fixed supports, about waist high. The spreaders are threaded on the wires and fastened in position. When the two-wire line is cut loose, it should be straight and taut.

The antenna is strung up in a straight line, or in an inverted V. An SWR curve should be run across each band, with the maximum indication less than 2:1. The SWR curve can be modified a bit by trimming or lengthening the wires in the stub.

Make sure your coax connection at the balun is waterproof to protect the line from internal moisture and corrosion.

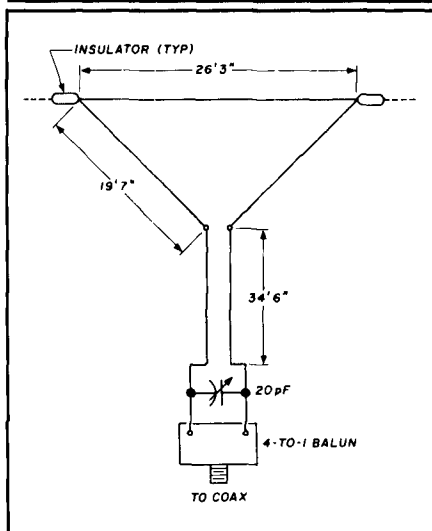
A delta loop for 7, 10, 14, 18, 21, 24, and 28 MHz

In a few months we'll finally have the 18-MHz band! This means there will be seven bands available between 7 and 29.7 MHz. It's time to think about a seven-band antenna.

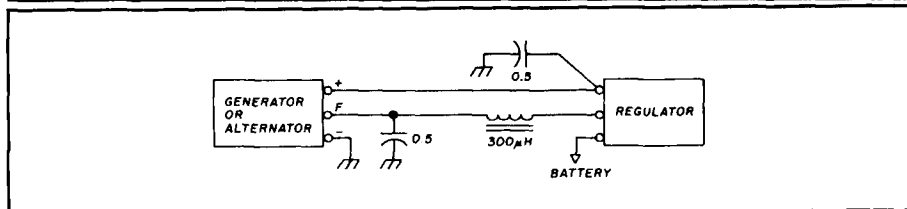
Why not try a center-fed antenna about 66 feet long in conjunction with a two-wire, balanced transmission line and an antenna tuner? How about using a delta loop in the same fashion

(fig. 5)? This particular design (attributed to Willi Richartz, HB9ADQ) is popular with many European stations. It's a loop configured so that the point of maximum current falls in the center of the top wire on the 7, 14, 21, and 28-MHz bands. If the open-wire feedline is cut to length as indicated, the loop may be fed on these bands with a 4:1 balun; no auxiliary tuner is required. A 20-pF capacitor is placed across the antenna feedpoints at the balun. It can be a ceramic or mica unit, or made up of a short length of 300-ohm line trimmed on a capacitance meter.

If you want to operate on 18 or 24 MHz, the antenna must be fed from a balanced tuner at the point where the

FIGURE 5

The HB9ADQ multiband delta-loop antenna. The feedline consists of no. 16 wire, spaced 4 inches. Spreaders are spaced 16 inches. Alternatively, 300-ohm ribbon line may be used, with an antenna tuner substituted for the 4:1 balun.

FIGURE 6

Alternator-generator noise may be substantially reduced by addition of filters, as shown in this simplified circuit. Capacitors are ordinary metal-cased "generator condensers." The 300- μ H choke must be capable of carrying the field current. (Circuit courtesy ZL2AJL.)

balun would be attached. The radiation pattern is a figure eight, at right angles to the plane of the loop. On 20 meters and the higher frequency bands, the loop provides a small gain over a dipole. For best operation, the top wire of the loop should be about 30 feet above ground.

More 88-mH inductors!

I just received a note from Ed Wetherhold, W3NQN (102 Archwood Avenue, Annapolis, Maryland 21401), telling me he has a quantity of 88-mH inductors suitable for use in audio filters and networks. If you're interested, send an SASE to Ed at the above address for more information.

Alternator or generator noise

A growing number of Amateurs are operating HF mobile after a lull in this activity for many years. There's still a problem with automobile electrical system noise, and some mobile operators are troubled by alternator or generator noise during reception.

In general, most alternator/generator noise or "whine" can be reduced (but not necessarily eliminated) by placing a 0.5- μ F coaxial capacitor on the output, or armature lead. Bypassing the field lead is, however, another matter. "Conventional wisdom" warns not to bypass this lead, or you may harm the voltage regulator unit.

Don Sutherland, ZL2AJL, takes exception to conventional wisdom in this case. He says the field wire may be bypassed to ground to eliminate noise, if the proper precautions are taken (fig. 6). A 300- μ H ferrite-core RF choke capable of carrying the field cur-

rent is placed in the lead, and the generator/alternator field wire is bypassed at the case of the unit. He says you'll have no difficulty with contact erosion in mechanical regulators, even with the relatively large value of bypass capacitor on the field lead, provided that you include the RF choke between the capacitor and the regulator. He notes that a British firm, Joseph Lucas (makers of automotive electrical equipment), has recommended this suppression technique for many years. Don says he developed the technique independently, with no knowledge of Lucas' prior work in that field.

The "Dead Band" Contest

Amazing, my dear Watson! More and more faithful readers of this column have correctly identified the quotation from the Sherlock Holmes story, "A Study in Scarlet." The sleuths include: Gerry Skloot, KE2N; Howard Tooker, W3TL; Ben Richardson, WB1CUA; Louis Axeman, Jr., N8LA; Dan Deckert, WA6FQC; Mike Mahoney, WA1KNO; and Chris Kirk, KA1RSV.

Since you're all such a smart bunch, Ed Wetherhold, W3NQN, offers this quiz: name the book, author, and the person to whom this quote is directed — "Call me Ishmael." Good luck!
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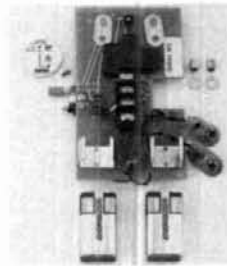
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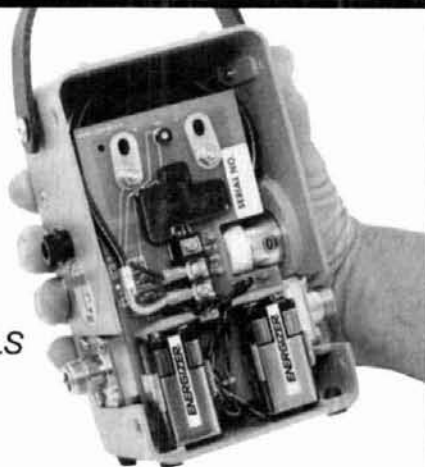
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THE HAM NOTEBOOK

Two in one: trace doubler for CRO, and square wave and pulse generator

My circuit (using one quad two-input NAND gate 4011 and one dual op amp LM358) is a simple, low cost, and easy-to-operate trace doubler for CROs. Other uses include: electronic switching, supplying blanking pulses for the z-axis of CROs, keying and synchronizing slave-type multivibrators and trigger circuits, adjusting the component values of CRO probes, and quick checking the frequency responses of amplifiers.

Circuit and working principle

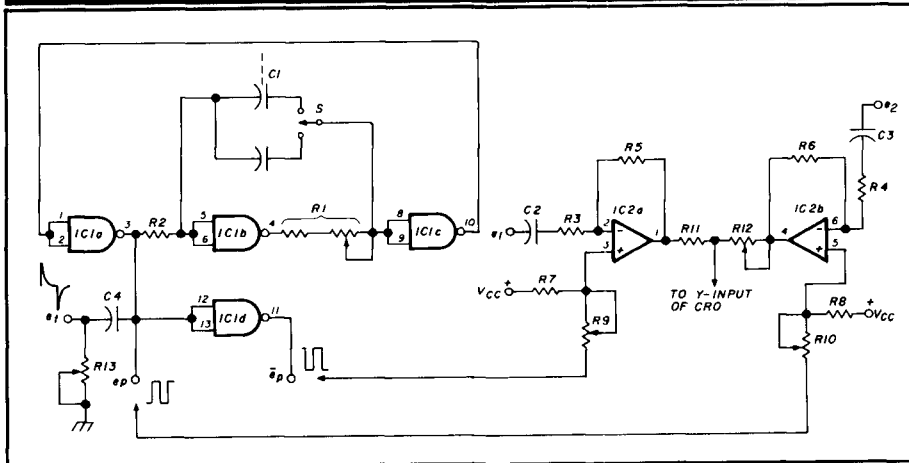
The trace-doubler circuit is shown in fig. 1. IC1a, IC1b, and IC1c of the

PARTS LIST

Parts List (fig. 1)

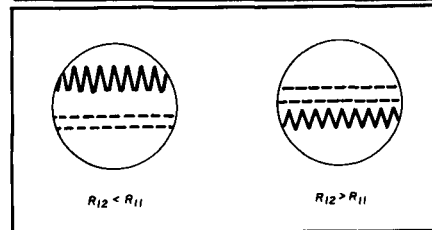
IC1	4011	R3	20k
IC2	LM358	R4	20k
C1	0.001 μ F	R5	200k
	0.01 μ F	R6	200k
	0.1 μ F	R7	50k
	1.0 μ F	R8	50k
	10 μ F	R9	50k pot
C2	25 μ F	R10	50k pot
C3	25 μ F	R11	100 ohm
C4	0.001 μ F	R12	300 ohm pot
		R13	50k pot
R1	500-ohm + 50-k pot	Vcc	6 volts
R2	500 ohm	S	multipole switch

FIGURE 1



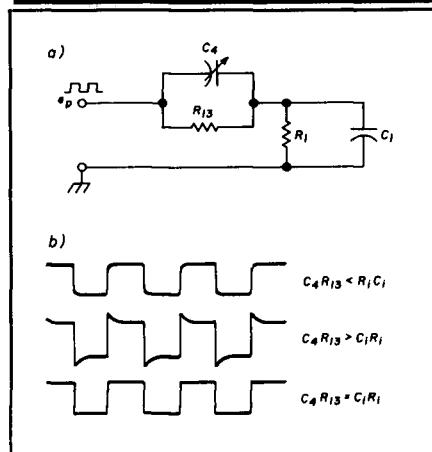
Circuit of the trace doubler for CRO, and square waves and pulse generator.

FIGURE 2



Oscilloscope screens showing input signals e_1 (sine wave) and e_2 (square wave). $R_{12} < R_{11}$ and $R_{12} > R_{11}$.

FIGURE 3



(A) Probe adjusting circuit for CRO. (B) Displayed square waves on CRO screen.

quad two-input NAND gate 4011 are connected as an astable multivibrator; IC1d is connected as an inverter. Terminals 3 and 11 of the 4011 give square waves with opposite phases. The square waves (e_p) at the output of IC1a, passing through differentiator C_4R_{13} , then form positive and negative pulses (e_t). The dual op amps of the LM358 are used as two gated amplifiers for the two signals e_1 and e_2 and fed through terminals 2 and 6, to be displayed simultaneously on the CRO screen.

The two opposite-phase square waves e_p and \bar{e}_p are used to gate IC2a and IC2b at terminals 3 and 5 of the LM358, respectively. Resistances R_9 and R_{10} are preadjusted so that one op amp is driven to saturation while the other works normally as an amplifier. Thus they will amplify the two signals e_1 and e_2 alternately, and two separate traces will be displayed on the screen. Resistance R_{12} can be varied to adjust

the vertical separation of the two traces.

Select a suitable value of C_1 with switch S and adjust the pot of R_1 . The frequency of square waves can be varied from 1 cps to 10^6 cps. This process is necessary for stabilizing the waveforms displayed on the screen.

A common supply of 6 volts is used in the circuit.

Practical examples

1. Figure 2 shows the oscillograms of the displayed input signals e_1 (sine wave) and e_2 (square wave).

2. Figure 3A is the probe adjusting circuit for CRO; fig. 3B shows the oscillograms of the displayed square waves of e_p at three different values of $R_p C_p$. R_1 is the input resistance of the CRO and C_i is the input capacitance.

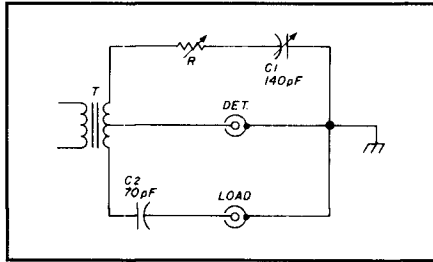
By Tseng C. Liao, Peking, China

Calibrating series-resistance capacitance bridges

Bridges like the series-resistance capacitance type shown in fig. 1 are easy to build and operate. But there seems to be some confusion about how to calibrate C_1 to indicate the correct load reactance. This confusion seems to result from the fact that there is a fixed capacitor C_2 in the load branch, and the signs in the formula used to determine the load reactance are opposite to those you'd expect.

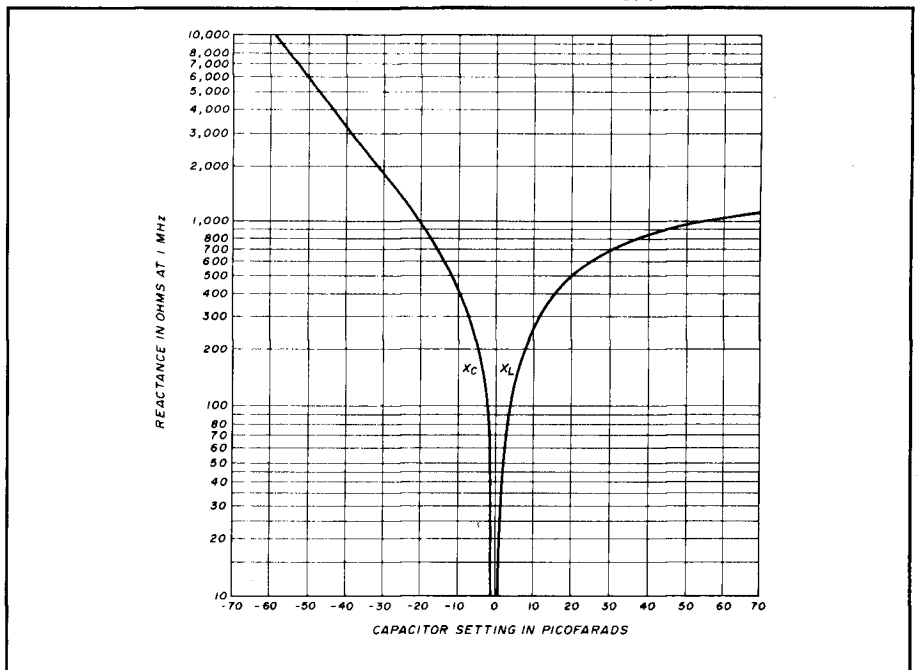
On the series-resistance capacitance bridge, C_2 is necessary because it permits nulling the bridge (zero load reactance) with C_1 set to the mid-position — namely, $C_1 = C_2 = 70$ pF. A capacitively reactive ($-X_x$) load allows nulling the bridge by reducing the capacitance of C_1 ; an inductively reactive ($+X_x$) load requires that C_1 be increased in value to do so. The equivalent series reactance ($\pm X_x$) of the unknown load impedance (Z_x) is the difference in the setting of C_1 between the initial balance when $X =$

FIGURE 1



Basic schematic of series-resistance-capacitance bridge.

FIGURE 2



Calibration curve for reactance.

0 ($C_1 = 70$ pF) and the load reactance, or

$$X_x = \frac{1}{2\pi F} \left(\frac{1}{C_1'} - \frac{1}{C_1''} \right)$$

where

C_1' is the first reading of $C_1 = 70$ pF
 C_1'' is the second reading of C_1 with the load

F is the test frequency.

A + sign indicates that X_x is capacitive, while a - sign corresponds to an inductive X_x . This appears to be a contradiction, but remember that C_1 is in the opposite branch of the bridge. To obtain the proper sign for the load reactance, simply reverse the sign in the answer.

A reactance plot of the capacitance of C_1 is shown in fig. 2 using eqn. 1 and a frequency of 1 MHz. To obtain the reactance at higher frequencies, divide the reactance for 1 MHz by the test frequency. The reactance plot is calibrated in capacitance in several steps from -70 pF through 0 pF to $+70$ pF, as shown.

In the event that C_1 is some value other than 140 pF, C_2 must be one-half that of C_1 . A smaller variable

capacitor will limit the useful reactance range of the bridge; a larger variable capacitor will reduce the accuracy of the bridge. The calibration procedure remains the same.

Wilfred N. Caron,
 Ridgecrest, California 93555
 Article D

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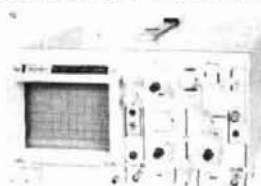
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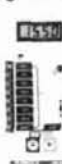
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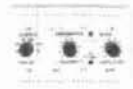
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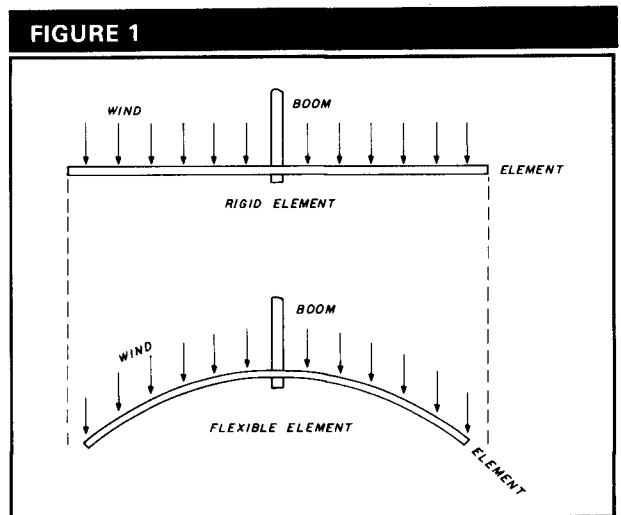
Try this simple analysis procedure

Over the past year or so, I've been working on a design procedure for developing structurally sound Yagi elements. I spent many hours with Bob Mitchell, N5RM, analyzing the structural integrity of his "Forty-Meter Flame Thrower" and developing the first steps of my procedure. After I completed my initial work, Gerald Williamson, K5GW, used the process to design the elements of two full-size 40-meter beams which are stacked on his rotating tower. He also used it to build his shortened-element 80-meter beam and is now designing a full-size 80-meter beam.

In late spring of 1987, I heard that Dick Fenwick, K5RR, had several identical Yagis elements break in high winds. I asked Dick to send me a sketch of the elements that failed, but not to tell me where they broke. After entering the data into my analysis program and letting it run, I found the element's weakness. Dick confirmed the correctness of my "after the fact" prediction. The elements of his identical beams failed at the exact spot the program indicated. This procedure should help you evaluate the mechanical integrity of your existing designs or design a homebrew Yagi.

Failure modes

An element has failed if it breaks off or is bent enough to render it useless. There are several causes of in-service failures. The element could be covered with too much ice, the wind hitting the element may impose a load which causes it to fail, or the element may break off because of wind-induced vibration or fluttering. The first two causes have to do with direct loading of the element due to ice and wind; the third generally happens at very



Graphic illustrations of both the Rigid Element Model and the Flexible Element Model, and how each reacts to a theoretical wind.

low wind speeds. My procedure deals only with the loading of the element, *not* with vibration-induced fatigue failures.

The environment and survivability

To determine survivability, give careful consideration to the Yagi's environment. The main environmental problem is loading due to ice and wind. The weight of the ice loads the element and its thickness increases the element diameter. The increased diameter of the element results in a higher wind load.

You must make several choices when designing or evaluating an element. It's necessary to determine or select the extreme ice and wind conditions the element will have to handle. Consider whether the element is expected to survive those conditions, or have an additional margin of safety. Some manufacturers state their



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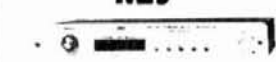


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design will survive specific wind speeds. In a strict engineering sense, survivability means that if the stated conditions are exceeded, there will be a failure. If there is a margin of safety, failure will occur at conditions of higher severity. It's wise to understand all aspects of the loads on an element, the materials used in its construction, and their safety factors. Without this, you could construct an element that costs and weighs more than it needs to survive its environment. This design might place unnecessarily higher loads on the tower and rotor.

Element analysis

You can mathematically construct two element models. I call them the Rigid Element Model (REM) and the Flexible Element Model (FEM). REM is an approximation of the more exact and complex FEM version. The REM model assumes the element doesn't deflect when loaded with ice or wind. It also assumes that all parts of the element are perpendicular to the wind. FEM accounts for the deflections of the element at all points along its length. The actual element length exposed to the wind decreases as it deflects. **Figure 1** shows the REM and FEM assumptions applied to an element. With FEM, the wind loading isn't perpendicular to the element at all points. This decreases the loading on the element as compared to REM. The wind loading of the element is less severe with FEM, but more accurate.

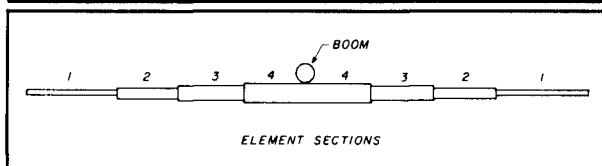
While the FEM version gives a precise description of the actual conditions, modeling is complex and time consuming. REM is easier and faster. The errors introduced by the REM assumptions result in a design more conservative than one using FEM.

General approach

Begin your element analysis by selecting the wind and ice conditions it is to survive and calculating the loads these conditions will place on the element. The loads are related to the element's size. You must know the relationship between the wind, ice, and tubing sizes used in the element to find the resulting loads. Once you've determined the loads, find the resulting stress by ascertaining the type of material used to make the element along with its geometric properties. Compare the stress to the maximum allowable value for the material used. If the resulting stress is lower than the maximum acceptable level, the design is conservative. If the stress is over the maximum acceptable level, the design won't survive the wind and ice conditions.

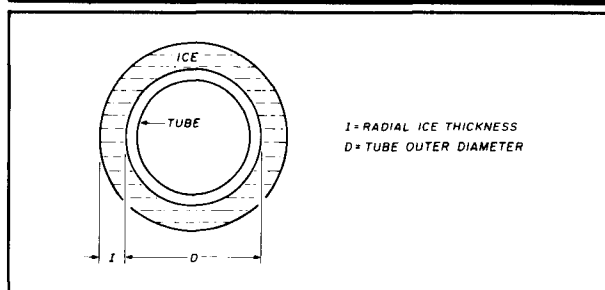
You can identify weak spots when analyzing an existing design or compare it with the relative merit of others. If an existing design is weak, you may choose to reinforce it or purchase another. When planning an element, you can alter the design by using different sizes and lengths of tubing in the element makeup until you find an acceptable combination.

FIGURE 2



A typical Yagi element constructed from telescoping sections of aluminum tubing.

FIGURE 3



Yagi element shown with "ice loading." If you know the tube outer diameter and the thickness of the ice on the element, you can closely approximate the amount of loading being placed on the element.

Element description

Figure 2 shows a typical element constructed from various tubing sizes. The outermost element section is called 1; the numbers increase as they approach the boom. Because the element is symmetrical relative to the boom, the other half of the element will have the same numbering scheme. An element section is a part of the element that has the same outer diameter and wall thickness. If one part of the element telescopes into another, a new section is formed. A section can be long or short, but its entire length must have the same wall thickness and outer diameter. If a tube is reinforced either on the outside or inside, a new section is created because its geometric properties are different. **Figure 2** shows a four-section element. Because the sections are the same on both sides of the boom, the analysis procedure will be applied only to one.

Element loading

There are three components to the loading of an element: the weight of any ice on the element section, the weight of the tubing making up the section, and the wind load on the section. They must be determined and summed to yield the total loading. The first step is to break the element into sections as shown in **fig. 2**. Then find the total load on each individual section.

Two types of ice can form on the element. The most common is solid ice; the least common is rime ice. My equations are based on solid ice weight. Solid ice weighs 56 pounds per cubic foot, rime ice about 30 pounds per cubic foot.² Generally, ice accumulation

on round tubes is stated in terms of "radial thickness." For example, if a 1-inch diameter tube has 0.25 inch of radial ice, the effective diameter for the wind loading is 1.5 inches. The inch weight is determined by the volume of ice surrounding the tube as shown in **fig. 3**.

For solid ice, W_i can be found using **eqn. 1**.

$$W_i = 0.102 \times L(D \times l + l^2) \quad (1)$$

W_i = weight of ice on section (pounds)

l = radial ice thickness (inch)

L = section length (inch)

D = tube outer diameter (inch)

To find the tubing weight in a section take one of two approaches. Either look up the weight of the tubing in a supplier's catalog or calculate it directly. The weight per foot is given on most tubing charts. Calculating the weight directly may be easiest because this method doesn't depend on having a catalog. Because most Yagi elements are made from aluminum tubing, use **eqn. 2** to find the section weight. This ignores the weight of the tubing inside the overlap of two telescoped sections.

$$W_a = 0.31 \times L(D \times T - T^2) \quad (2)$$

W_a = weight of aluminum tubing section (pounds)

T = tubing wall thickness (inch)

L = section length (inch)

D = tube outer diameter (inch)

The last load on the element section is wind induced. When the wind strikes a surface, pressure is created by the impact of the air stream on the surface. The wind load depends mainly on the wind velocity and the shape of the impacted surface; some shapes are more or less streamlined than others. Use **eqn. 3** to find the wind load on a round tubing section. The drag coefficient is included in the equation to account for the streamlined effect of a round tube,² along with the conversion of units for wind pressure.

$$F_w = 0.0047 \times L \times D_e \times P \quad (3)$$

F_w = wind load on round section (pounds)

L = section length (inch)

P = wind pressure perpendicular to a flat surface (pounds/square foot)

D_e = effective outer diameter of tube (inch)

The effective diameter of the tube (D_e) accounts for an increase in diameter due to ice. If there's no ice, the tube's outer and effective diameter are the same.

$$D_e = D + l + l \quad (4)$$

D_e = effective outer diameter of tube (inch)

l = radial ice thickness (inch)

D = tube outer diameter (inch)

The total load on a section (F_t) is the sum of the ice weight, element weight, and wind load.

$$F_t = W_i + W_a + F_w \quad (5)$$

F_t = total load on section (pounds)

W_i = weight of ice on section (pounds)

W_a = weight of aluminum tubing section (pounds)

F_w = wind load on section (pounds)

You could argue that the two weights added together are at right angles to the wind load and shouldn't be added directly. There's no guarantee that this will be the case; upward and downward wind streams are a common occurrence.³

Wind pressure

Calculate the wind pressure striking a flat surface with **eqn. 6**.² This isn't the wind pressure on a round tube, but a flat surface. **Equation 3** includes a "drag coefficient" to alter the wind pressure found in **eqn. 6**. **Equation 6** also includes a gust factor of 1.30 to account for short duration gusts peaking above the mean speed of V . If you select a wind speed and use **eqn. 6**, you are actually calculating for a wind speed 1.30 times higher. For example, when you select a wind speed of 86.6 mph, you are actually accounting for a peak wind of 112.6 mph.

$$P = 0.004 \times V^2 \quad (6)$$

P = wind pressure on flat surface with 1.30 gust factor (pounds/square foot)

V = wind speed (miles/hour)

If you don't want to use a gust factor, you can modify **eqn. 6** to find the wind pressure at the exact wind speed entered. Removing the gust factor gives you **eqn. 7**.

$$P = 0.0024 \times V^2 \quad (7)$$

P = wind pressure on flat surface (pounds/square foot)

V = wind speed (miles/hour)

What's the proper wind load an element should be expected to handle? You can make the selection in several ways. Research the history of wind speeds in your area. Go back about 20 to 50 years to see what the worst wind has been. Find out if the wind information should have the gust factor applied.

Consult local building codes covering towers and similar structures. EIA standard RS 222c contains information on the wind loading towers should be designed to handle, based on their geographical location. You can also consult the American Standard Building Code. Both EIA RS 222c and the American Standard Building Code include maps of the United States recommending design wind loads. There are small differences between the codes, but for Amateur applications they are basically the same.

According to RS 222c, most of the United States should expect a 50-year mean reoccurrence wind of 86.6 mph. Certain coastal areas have a 100 mph or higher recommendation. The wind speeds found in EIA RS 222c are mean wind speeds, and are to be used with **eqn. 6**. The most common wind speed is 86.6 mph; 100.0 and 112.0 mph are the extreme values. **Table 1** shows wind pressures at various mean wind speeds and their corresponding peak value with a 1.30 gust factor.

Because the REM procedure errs on the conservative side, using a mean wind speed of 86.6 mph results in a conservative design for most areas and would be a rigid

TABLE 1

Wind pressures at various mean wind speeds and their corresponding peak value with a 1.30 gust factor.

Mean Wind Speed (mph)	Corresponding peak wind with 1.30 gust factor (mph)	Wind pressure (pounds/square foot)
20.0	26.0	1.6
30.0	39.0	3.6
40.0	52.0	6.4
50.0	65.0	10.0
60.0	78.0	14.4
70.0	91.0	19.6
80.0	104.0	25.6
86.6	113.0	30.0
100.0	130.0	40.0
112.0	145.6	50.0
115.0	149.5	52.9
125.0	162.5	62.5

TABLE 2

Calculate the worst combinations of conditions in your area for winter and non-winter conditions to evaluate existing design. Numbers shown are for my QTH.

Season	Radial ice	Mean wind	Peak wind	Pressure level
Winter	0.25 inch	40.0 mph	52 mph	6.4 pounds/square foot
Non-winter	0 inch	86.6 mph	113 mph	30 pounds/square foot

TABLE 3

Dimensions for half of a 36-foot Yagi element with four sections as in *fig. 2*.

Section	L (inch)	D (inch)	T (inch)
1	48.0	0.500	0.058
2	60.0	0.625	0.058
3	72.0	0.750	0.058
4	36.0	0.875	0.058

TABLE 4

Winter conditions

Section	Wi (pounds)	Wa (pounds)	Fw (pounds)	Ft (pounds)
1	0.92	0.39	1.45	2.76
2	1.34	0.61	2.04	3.99
3	1.83	0.90	2.71	5.44
4	1.04	0.53	1.49	3.06

TABLE 5

Non-winter conditions

Section	Wi (pounds)	Wa (pounds)	Fw (pounds)	Ft (pounds)
1	0	0.39	3.38	3.77
2	0	0.61	5.29	5.90
3	0	0.90	7.61	8.51
4	0	0.53	4.44	4.97

standard by which to evaluate existing designs. Judge the expected amount of radial ice and, more importantly, the combination of wind and ice for your own area and make your evaluations based on these sets of conditions. Here in northern Texas, our highest winds occur in the spring and early summer. We often have ice

storms in the winter, but the winds are not very high. At my location I use the two sets of conditions in **table 2**; yours may be quite different.

Loading example

Table 3 gives the dimensions for half of a 36-foot Yagi

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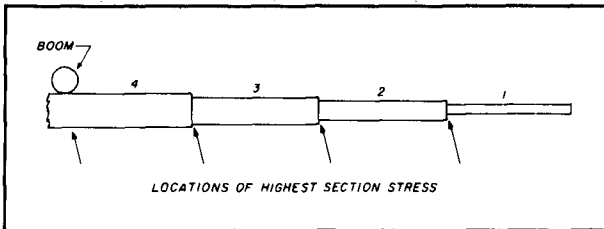
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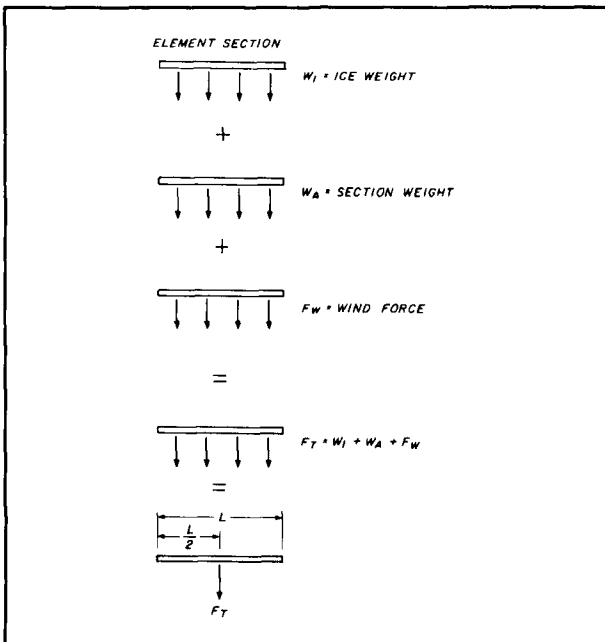
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FIGURE 4



The joints where progressive sections of an element telescope together are typically the high stress points along the element.

FIGURE 5



Shown here are the three individual distributed forces, the total distributed force, and the total force applied at the element's "center of action."

element with four sections like those in **fig. 2**. **Tables 4 and 5** show the loads W_i , W_a , F_w , and F_t for the winter and non-winter conditions in **table 2**. Comparing the F_t s for both cases shows the non-winter conditions to be much more severe than the winter ones. Because the non-winter conditions are the most severe, only they will be used in the last stages of the element analysis. When confronted with several sets of conditions, determine which are the most severe and use them in your analysis.

The stress in a section varies along the section length. The highest value occurs at the point where one section ends and another begins, as you approach the boom. In this analysis procedure, you'll calculate only the highest stress value in each section. **Figure 4** shows the locations under the greatest stress in a four-section element.

The forces resulting from wind, ice weight, and element weight of each section are evenly distributed over the section's length. The three evenly distributed forces can be replaced by a point force (F_t) applied at a unique

location. The location is at the "center of action" — the section's midpoint. **Figure 5** shows the three individual distributed forces, the total distributed force, and the total force applied at its center of action. You need F_t s and their points of application to find the maximum stress in the sections.

F_t s cause the element to bend; this results in bending stresses in the tube sections. These stresses are calculated from the geometry of the tube and the amount of bending action. Use **eqn. 8** to find the bending stress when you know the section modulus of the tube and the bending moment at the point of interest. There is another stress at this point, but it's very small and will be ignored.

$$S_b = \frac{M}{Z} \quad (8)$$

S_b = bending stress (pounds per square inch, psi)

M = bending moment (pound per inch)

Z = section modulus (inch³)

The section modulus for a round tube (Z) can be found using **eqn. 9**.

$$Z = 0.098 \times \frac{D^4 - (D - 2T)^4}{D} \quad (9)$$

Z = section modulus (inch³)

D = tube outer diameter (inch)

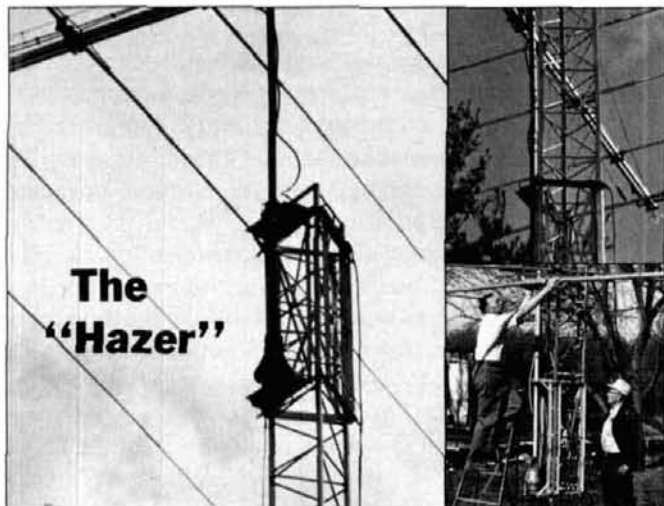
T = tube wall thickness (inch)

The section modulus describes the geometry of the tube. If you consider tubes of the same material, the one with the larger section modulus can take additional bending. To find the section modulus for two or more close-fitting telescoped tubes, make the combined wall thickness T and the largest outer diameter D . **Table 6** gives the section moduli for a number of tube sizes. **Table 7** gives the section moduli for various telescoped combinations.

In **table 7**, the combined wall thickness of 0.116 inch is for two walls of 0.058 inch; the combined wall thickness of 0.174 inch is for three walls of 0.058 inch. The values shown are for standard telescoping combinations. For example, an 0.875 inch outer diameter tube with a combined wall thickness of 0.174 inch is made of three telescoped tubes. It has 0.875, 0.750, and 0.500-inch diameter tubes, each with a wall thickness of 0.058 inch.

To find the bending moment you must know the forces causing the bending and the distances to their points of application. The forces are the F_t s found for each section; the distances are taken from the location of the section midpoints. **Figure 6A** shows the situation for section 1. Find the moment at the point of maximum stress in section 1 with **eqn. 10**.

$$M_1 = F_t l \times \frac{L_1}{2} \quad (10)$$



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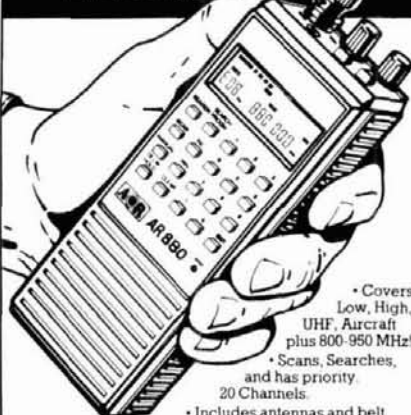
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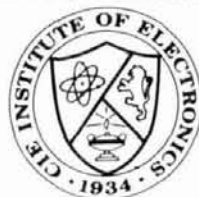


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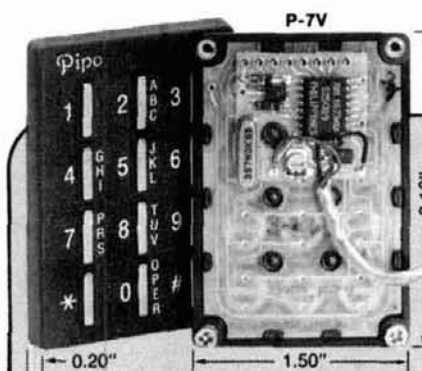
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TABLE 6

Section moduli and weights for a number of tube sizes.

Tube outer diameter (inch)	Wall thickness (inch)	Weight per foot (lbs/ft)	Section modulus (inch ³)
0.25	0.035	0.03	0.0011
0.25	0.049	0.04	0.0013
0.25	0.058	0.04	0.0014
0.375	0.049	0.06	0.0036
0.375	0.058	0.07	0.0040
0.50	0.058	0.01	0.0080
0.50	0.125	0.17	0.0115
0.625	0.058	0.12	0.0134
0.625	0.125	0.23	0.0208
0.75	0.058	0.15	0.0202
0.75	0.125	0.	0.0332
0.875	0.058	0.18	0.0285
0.875	0.120	0.34	0.0474
1.00	0.058	0.20	0.0382
1.00	0.125	0.40	0.0670
1.125	0.058	0.23	0.0492
1.125	0.125	0.46	0.0885
1.25	0.058	0.26	0.0618
1.25	0.125	0.52	0.1130

TABLE 7

Section moduli for various telescoped combinations.

Tube outer diameter (inch)	Combined wall thickness (inch)	Section Modulus (inch ³)
0.375	0.116	0.0051
0.500	0.116	0.0112
0.500	0.174	0.0120
0.625	0.116	0.0202
0.625	0.174	0.0230
0.750	0.116	0.0319
0.750	0.174	0.0379
0.875	0.116	0.0465
0.875	0.174	0.0570
1.000	0.116	0.0639
1.000	0.174	0.0803
1.125	0.116	0.0841
1.125	0.174	0.1078
1.250	0.116	0.1072
1.250	0.174	0.1395

M1 = moment in section 1 (pound-inch)

Ft1 = total load on section 1 (pounds)

L1 = length of section 1 (inch)

Using the non-winter conditions of **table 5**, calculate the bending moment and bending stress for section 1 as follows:

From **table 5**, Ft1 = 3.77 pounds

From **table 3**:

L1 = 48.0 inches

D1 = 0.500 inch

T1 = 0.058 inch

and then from **table 6**

Z1 = 0.0080 inch³

Using **eqn. 10**

$$M1 = 3.77 \text{ pounds} \times \frac{48.0}{2} \text{ inch} = 90.5 \text{ pound-inch}$$

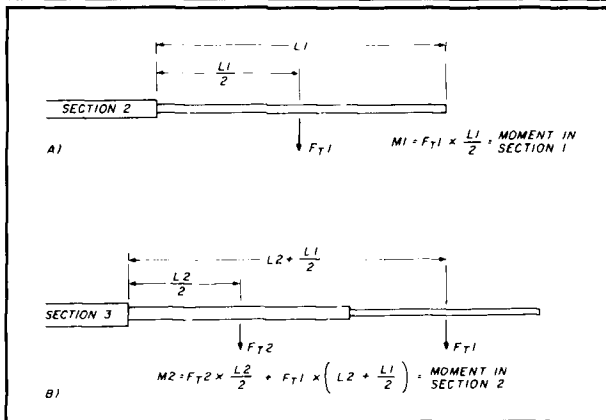
Using the bending moment and the section modulus (Z1) calculate the bending stress using **eqn. 8**.

$$Sb1 = \frac{90.5 \text{ pound-inch}}{0.0080 \text{ inch}^3} = \frac{11,312.5 \text{ pounds}}{\text{inch}^2}$$

Or 11,312.5 psi

Sb1 = bending stress for section 1 (pounds per square inch)

FIGURE 6



(A) Determining the moment for section one of the element.
 (B) Determining the moment for section two, and showing how the moment of the previous section(s) are added together for each new section calculated.

To find the bending moment at the highest stress point in section 2, multiply the appropriate F_t s by the distance from their centers of action to the highest stress point and then add them together. **Figure 6B** shows the forces and distances. M_2 is the sum of the moments produced by F_{t1} and F_{t2} .

$$M_2 = F_{t2} \times \frac{L_2}{2} + F_{t1} \times \left(L_2 + \frac{L_1}{2} \right) \quad (11)$$

M_2 = bending moment at end of section 2 (pound-inch)

F_{t2} = section 2 total load (pounds)

F_{t1} = section 1 total load (pounds)

L_1 = section 1 length (inch)

L_2 = section 2 length (inch)

Find the stress in section 2 with **eqn. 8** using the moment at the point of highest stress and the section modulus at that point.

$$S_{b2} = \frac{M_2}{Z_2}$$

Continuing with the values from **table 3** and the non-winter case from **table 5**, the variables are as listed:

L_1 = 48.0 inches

L_2 = 60.0 inches

F_{t1} = 3.77 pounds

F_{t2} = 5.91 pounds

D_2 = 0.625 inch

T_2 = 0.058 inch

Z_2 = 0.0134 inch³ (from **table 6**)

$$M_2 = 5.91 \text{ pounds} \times \frac{60.0}{2} \text{ inch} + 3.77 \text{ pounds} \times \left(60.0 \text{ inch} + \frac{48.0}{2} \text{ inch} \right)$$

$$M_2 = 177.3 \text{ pound-inch} + 316.7 \text{ pound-inch} = 494.0 \text{ pound-inch}$$

$$S_{b2} = \frac{M_2}{Z_2} = \frac{494.0 \text{ pound-inch}}{0.0134 \text{ inch}^3} = 36,865.6 \text{ PSI}$$

If there are three sections, M_3 is calculated from:

$$M_3 = F_{t3} \times \frac{L_3}{2} + F_{t2} \times \left(L_3 + \frac{L_2}{2} \right) + F_{t1} \times \left(L_3 + L_2 + \frac{L_1}{2} \right)$$

$$S_{b3} = \frac{M_3}{Z_3}$$

If there are four sections, M_4 is calculated from:

$$M_4 = F_{t4} \times \frac{L_4}{2} + F_{t3} \times \left(L_4 + \frac{L_3}{2} \right) + F_{t2} \times \left(L_4 + L_3 + \frac{L_2}{2} \right) + F_{t1} \times \left(L_4 + L_3 + L_2 + \frac{L_1}{2} \right)$$

$$S_{b4} = \frac{M_4}{Z_4}$$

If there are more than four sections, the method is expanded following the same pattern. Use what follows as a guide.

The highest stress in a section is determined by finding the bending moment at the point of highest stress and dividing it by the section modulus of the tube at that point. The bending moment is found by multiplying the forces (F_t s) causing the bending at the point of highest stress by the corresponding distance to their points of application and then summing.

At this point, it's easier to either write a program to do all the math, or do it by hand in tabular form. **Table 8** shows the complete solution set for the example being used.

The maximum stress in each section has been calculated and must be compared to the allowable maximum. There are three popular aluminum alloys used in commercial Yagis and by Amateur builders. The maximum allowable stress for each is shown in **table 9**. The most commonly used alloy, 6061-T6, is found in most commercial Yagis; it can be obtained from supply houses and mail-order outlets.

The maximum allowable stress is usually called the "yield stress." Exceed this stress level and the part may break or be permanently bent. If you go beyond this level only slightly, you may not notice the bend because of the existing element droop. But if you greatly exceed the stress level, your element may incur a large, permanent bend or break. In this situation, a hidden safety factor

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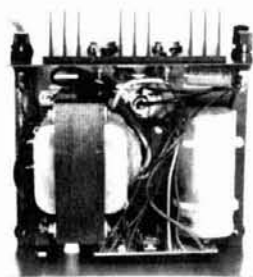
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MODEL RS-50A



MODEL RS-50M



MODEL VS-50M

RM SERIES



MODEL RM-35M

19" x 5 1/4" RACK MOUNT POWER SUPPLIES

MODEL	Continuous Duty (Amps)	ICS* (Amps)	Size (IN) H x W x D	Shipping Wt. (lbs.)
RM-12A	9	12	5 1/4 x 19 x 8 1/4	16
RM-35A	25	35	5 1/4 x 19 x 12 1/2	38
RM-50A	37	50	5 1/4 x 19 x 12 1/2	50
• Separate Volt and Amp Meters				
RM-12M	9	12	5 1/4 x 19 x 8 1/4	16
RM-35M	25	35	5 1/4 x 19 x 12 1/2	38
RM-50M	37	50	5 1/4 x 19 x 12 1/2	50

RS-A SERIES



MODEL RS-7A

MODEL	Continuous Duty (Amps)	ICS* (Amps)	Size (IN) H x W x D	Shipping Wt. (lbs.)
RS-3A	2.5	3	3 x 4 3/4 x 5 3/4	4
RS-4A	3	4	3 3/4 x 6 1/2 x 9	5
RS-5A	4	5	3 3/4 x 6 1/2 x 7 1/4	7
RS-7A	5	7	3 3/4 x 6 1/2 x 9	9
RS-7B	5	7	4 x 7 1/2 x 10 1/4	10
RS-10A	7.5	10	4 x 7 1/2 x 10 1/4	11
RS-12A	9	12	4 1/2 x 8 x 9	13
RS-12B	9	12	4 x 7 1/2 x 10 1/4	13
RS-20A	16	20	5 x 9 x 10 1/2	18
RS-35A	25	35	5 x 11 x 11	27
RS-50A	37	50	6 x 13 3/4 x 11	46

RS-M SERIES



MODEL RS-35M

MODEL	Continuous Duty (Amps)	ICS* (Amps)	Size (IN) H x W x D	Shipping Wt. (lbs.)
• Switchable volt and Amp meter				
RS-12M	9	12	4 1/2 x 8 x 9	13
• Separate volt and Amp meters				
RS-20M	16	20	5 x 9 x 10 1/2	18
RS-35M	25	35	5 x 11 x 11	27
RS-50M	37	50	6 x 13 3/4 x 11	46

VS-M AND VRM-M SERIES



MODEL VS-35M

- Separate Volt and Amp Meters • Output Voltage adjustable from 2-15 volts • Current limit adjustable from 1.5 amps to Full Load

MODEL	Continuous Duty (Amps)			ICS* (Amps)	Size (IN) H x W x D	Shipping Wt. (lbs.)
	@13.8VDC	@10VDC	@5VDC	@13.8V		
VS-12M	9	5	2	12	4 1/2 x 8 x 9	13
VS-20M	16	9	4	20	5 x 9 x 10 1/2	20
VS-35M	25	15	7	35	5 x 11 x 11	29
VS-50M	37	22	10	50	6 x 13 3/4 x 11	46
• Variable rack mount power supplies						
VRM-35M	25	15	7	35	5 1/4 x 19 x 12 1/2	38
VRM-50M	37	22	10	50	5 1/4 x 19 x 12 1/2	50

RS-S SERIES



MODEL RS-12S

- Built in speaker

MODEL	Continuous Duty (Amps)	ICS* (Amps)	Size (IN) H x W x D	Shipping Wt. (lbs.)
RS-7S	5	7	4 x 7 1/2 x 10 1/4	10
RS-10S	7.5	10	4 x 7 1/2 x 10 1/4	12
RS-12S	9	12	4 1/2 x 8 x 9	13
RS-20S	16	20	5 x 9 x 10 1/2	18

TABLE 8

Complete solution set.

Sec	OD (in)	T (in)	L (in)	Ft (lbs)	Z (in ³)	M (lbs-in)	Sb (psi)
1	0.500	0.058	48.0	3.77	0.0081	90.5	11,300
2	0.625	0.058	60.0	5.90	0.0134	494.0	36,860
3	0.750	0.058	72.0	8.51	0.0202	1496.3	74,070
4	0.875	0.058	36.0	4.97	0.0285	2240.2	78,600

TABLE 9

Maximum allowable stress for the three popular aluminum alloys used in commercial Yagis and by Amateur builders.

Aluminum Alloy	Maximum allowable stress (psi) (4)
6061-T6	35,000
6063-T6	25,000
6063-T83	30,000

TABLE 10

Element with section lengths altered to obtain maximum allowable stress.

Sec	OD (in)	T (in)	L (in)	Ft (lbs)	Z (in ³)	M (lbs-in)	Sb (psi)
1	0.500	0.058	84.0	6.59	0.0081	276.7	34,580
2	0.625	0.058	24.0	2.36	0.0134	463.2	34,500
3	0.750	0.058	24.0	2.84	0.0202	712.0	35,130
4	0.875	0.058	84.0	11.69	0.0285	2189.0	76,720

TABLE 11

Element with section 4 a telescoped combination 1.00 and 0.875-inch diameter tube.

Sec	OD (in)	T (in)	L (in)	Ft (lbs)	Z (in ³)	M (lbs-in)	Sb (psi)
1	0.500	0.058	84.0	6.59	0.0081	276.7	34,580
2	0.625	0.058	24.0	2.36	0.0134	463.2	34,500
3	0.750	0.058	24.0	2.84	0.0202	712.0	35,130
4	1.000	0.116	84.0	14.51	0.0640	2311.5	36,110

may come into play. If the maximum allowable stress is just slightly surpassed, you may not have a failure resulting in element breakage. The only result may be a slight permanent bend, which may not be observable or cause any harm. This safety factor would come into play if the peak wind conditions were exceeded.

The example in **table 8** shows that, regardless of the alloy used, this design is over stressed in two areas. In addition, it's marginal in one area and acceptable in another. Using 6061-T6 aluminum throughout this example, the maximum allowable stress is 35,000 psi. Any section stress below this value indicates a section which is not fully utilized; any section stress above the maximum value indicates a section which is overloaded. An overloaded section must be changed to bring the stress level down to an acceptable level. You'll have equal strength when all section stresses have the same value. There are good reasons to have some sections stronger than others, but this is an economic decision to be discussed later.

What can be done to improve the example element in **table 8**? Make the 0.500 diameter tube longer to take more load and reduce the length of others while keeping the total length the same. Lengthening the 0.500 diameter tube to allow it to take more load also reduces the total wind load put into the element because the smaller diameter tubing is replacing the larger. **Table 10** shows the same element with altered section lengths. Starting at the outer section and working towards the boom, the section lengths were changed to obtain the maximum allowable stress.

Sections 1, 2, and 3 are acceptable; 4 is still unacceptable. There will be slight improvement if you use more of the lighter, less expensive tubing. Section 4 still has a problem, but has improved somewhat. With the smaller sections optimized, improvement in section 4 is impossible without a change in its geometry. **Table 11** shows the same element, with section 4 as a telescoped combination of 1.00 and 0.875-inch diameter tubes.

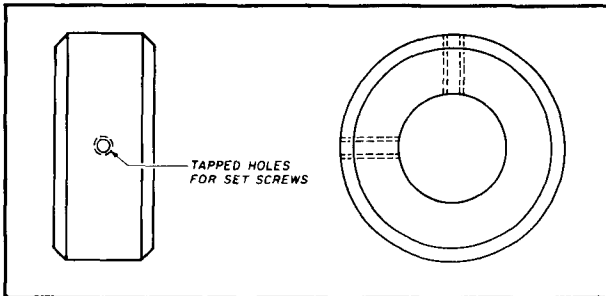
Section 4 has a stress slightly over the maximum. This

TABLE 12

Example of section 4 shown as a single tube with marginal strength.

Sec	OD (in)	T (in)	L (in)	Ft (lbs)	Z (in ³)	M (lbs-in)	Sb (psi)
1	0.500	0.058	84.0	6.59	0.0081	276.7	34,580
2	0.625	0.058	24.0	2.36	0.0134	463.2	34,500
3	0.750	0.058	24.0	2.84	0.0202	712.0	35,130
4	1.250	0.058	84.0	16.60	0.0619	2399.4	38,780

FIGURE 7



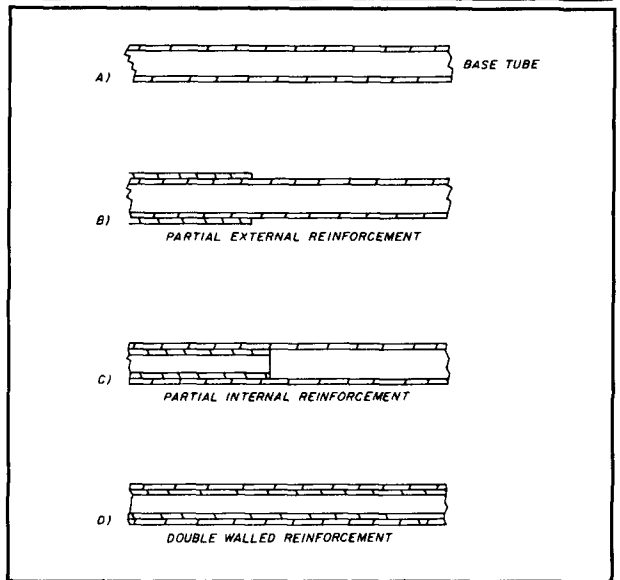
Description of a spacer which can be used when making a large decrease in tubing sizes on an element; i.e., two sizes that will not telescope together and allow a compression joint.

design is totally acceptable given the conservative nature of the rigid element model. There are several things to note. As the element gets longer, the strength requirements rapidly increase. This can be seen by the very short lengths of sections 2 and 3. In addition, section 4 had to be drastically reinforced. Table 12 shows the same example, where section 4 is a single tube with marginal strength. Section 4 is a 1.250-inch diameter tube of 0.058-inch wall thickness. This large tube has about the same section modulus as the composite of the 1.000 and 0.875-inch tubes, but has a larger wind load due to its larger diameter. This offsets some of its greater load bearing capacity.

You'll encounter a problem when making a large jump in tubing size. Because the jump from 0.750 to 1.250 isn't a telescoping fit, you need to fabricate a spacer or "donut." Figure 7 shows a spacer used by N5RM to build his 40-meter flame thrower.¹ Several manufacturers swage the end of a larger tube to a smaller size. The result is a large diameter reduction allowing a telescoping fit with a smaller tube. This method is not practical for the individual builder.

There are several ways to achieve a significant increase in section strength. One is to try increasingly larger diameter tubes in your calculations, until you find an outcome with an acceptable stress. This could lead to a fabrication problem due to non-telescoping tubing sections. You can also increase the strength of a section by externally or internally reinforcing the tube along part or all of its length. Figure 8 shows three reinforcement methods. In doing the analysis, you will create a new section when there is a change in the tube geometry.

FIGURE 8



Several methods for reinforcing element tubing are shown: At (A) the base tube with no reinforcing, at (B) the base tube with partial external reinforcement, at (C) the base tube with partial internal reinforcement, and at (D) the base tube as used in a double walled reinforcement.

Figures 8A and 8D are one section while figs. 8B and 8C are two sections. The method you select should be based on cost, ease of construction, availability of materials, total element weight, and total element wind area. There are a large number of possible combinations of tubing sizes which can be successfully used in a design. The final configuration depends on your resources and ingenuity.

It's desirable to have a design with no weak links, but having links of different strengths can be good and bad. It depends on what you want the design to accomplish. If you want the absolutely lightest element, design sections with the same maximum allowable stress. This design may not provide an economical use of tubing; it's usually purchased in finite lengths, and sections may be wasted. Zero waste may not be possible unless you make it a design consideration from the beginning. You could try to put together an element without cutting tubing which could be used for another project. In this case the section stresses might be quite different. This is totally acceptable provided none exceed the maxi-

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MJE2955T	PNP	TO-220	75 each
MJE3055T	NPN	TO-220	75 each
TIP30	NPN	TO-220	75 each
TIP31	NPN	TO-220	75 each
TIP32	NPN	TO-220	75 each
TIP41	NPN	TO-220	75 each
TIP42	PNP	TO-220	75 each
TIP121	NPN	TO-220	75each
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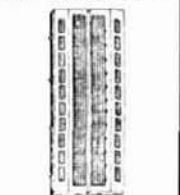
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TABLE 13

Tubing sizes of a 36-foot element with poor design.				
Section	EWT = 8.4 pounds		EWL = 68.4 pounds	
	D (inch)	T (inch)	L (inch)	Sb (psi)
1	1.000	0.058	48.00	4,760
2	1.125	0.058	96.00	35,050
3	1.250	0.058	72.00	64,910

TABLE 14

36-foot element with improved design.				
Section	EWT = 8.0 pounds		EWL = 66.4 pounds	
	D (inch)	T (inch)	L (inch)	Sb (psi)
1	1.000	0.058	131.00	35,450
2	1.125	0.058	13.00	33,220
3	1.250	0.058	18.00	33,700
4	1.250	0.116	54.00	35,830

TABLE 15

Comparison of materials used in Tables 13 and 14.				
Tube Diameter size (0.058 wall)	Case 1 (Table 13)		Case 2 (Table 14)	
	12-foot lengths needed	waste	12-foot lengths needed	waste
1.000	1	38 inches	2	16 inches
1.125	2	86 inches	1	0 inches
1.250	1	0 inches	1	0 inches

mum allowable stress. You can use different alloys of tubing as long as you don't exceed the maximum allowable stress level for each type.

The section nearest the boom will be the most expensive and minimum waste is a goal. Make section 1 from the least costly tubing. It can give you the largest span for the least money. Look closest at the intermediate sections for waste. Several other considerations mentioned earlier come into play when making tradeoffs between tubing sizes and reinforcement methods. Consider the overall element weight and area. If there is choice between several options, the lighter, smaller area element offers some advantages. If two designs for a four-element, 20-meter beam were found to have acceptable stress levels, choose between them on basis of the amount of wind load they put into the tower and rotator. Because using REM requires finding the weight and wind load of each section, it would be easy to sum the total section weights and wind loads to obtain two other parameters for comparing element designs. Multiply these by 2 to obtain the total for both element halves.

$$EWT = 2 \times (\text{sum of all section } W_{as}) \quad (12)$$

= total element weight (pounds) ignoring overlap

$$EWL = 2 \times (\text{sum of all section } F_{ws}) \quad (13)$$

= total wind load on element (pounds) at maximum wind speed

I found the element design in table 13 in an Amateur publication. The tubing sizes for this 36-foot element show that it is a very strong one. Or is it? With the analysis done at 86.6 mph and no ice, this element was found to be poor and the end of section 3 to be very weak. Section 1 could be made a lot longer. I found an acceptable configuration after I made several attempts to improve this design using the same tube sizes. Table 14 shows the improved design.

Section 1 was greatly lengthened, while section 2 was greatly reduced. Section 3 was changed to a shorter section. The new section 4 is the remainder of the old section 3, reinforced on the inside with some of the same material used in section 2. Not only has the strength of the element improved, but there has been a slight drop in element weight and wind load. Was this an efficient use of the material? Table 15 shows the materials used and the waste for the two cases. This was done assuming a 5-inch overlap at each joint and stock tubing lengths of 12 feet. You can make several conclusions when comparing the published design and improved version by looking at

TABLE 16

Revised element for improved design.

Section	EWT = 7.3 pounds		EWL = 42.8 pounds	
	D (inch)	T (inch)	L (inch)	Sb (psi)
1	0.500	0.058	84.00	34,580
2	0.625	0.058	24.00	34,500
3	0.750	0.058	23.00	34,550
4	0.750	0.116	30.00	34,640
5	1.00	0.116	55.00	34,730

TABLE 17

Summary of features of element designs in *Tables 16, 13, and 14.*

	Table 16	Table 13	Table 14
Survival mean wind speed (peak) (mph)	86.6 (112.5)	64.0 (83.2)	86.6 (112.50)
Element weight (pounds)	7.3	8.4	8.0
Element wind load at 86.6 mph (pounds)	42.8	68.4	66.4

tables 13, 14, and 15. The improved version is lighter, less expensive to build, places less wind load on the tower, and is significantly stronger.

Take care not to generate a design with a hidden problem. The example in **table 11** is a buildable design, but has a construction problem. Section 4 is 84 inches long. This is not half of a 12-foot piece where 6 feet are used on each side of the boom. Using the 84-inch section results in a lot of waste, and requires special efforts for mounting and joining at the boom. A design revision uses a piece of section 2 material for internal reinforcement. Two 12-foot telescoped pieces are cut to a length of 110.0 inches with half on each side of the boom. **Table 16** shows the improved design.

Table 17 summarizes the features for the element designs in **tables 16, 13,** and **table 13's** improved version in **table 14.** This improvement costs less and is slightly lower in weight and wind load. The element in **table 16** will withstand the same wind, but have about 35 percent less wind load. You can build Yagis which minimize the loads placed on towers, booms, and rotators, while still surviving very high winds.

Before using this method of element design, determine your constraints, limitations, and objectives. The

procedure allows you to generate designs to minimize weight and wind loading, and make optimal use of materials. It can be used to evaluate any existing design.

Summary

This analysis procedure provides a simple and sound method to evaluate the structural integrity of existing element designs and assist in the process of designing an element. I have presented several methods of reinforcing element sections and various criteria by which to judge them. To implement the procedure, you'll need to determine the *worst set of survival conditions for your geographical location, your objectives, and restrictions.*

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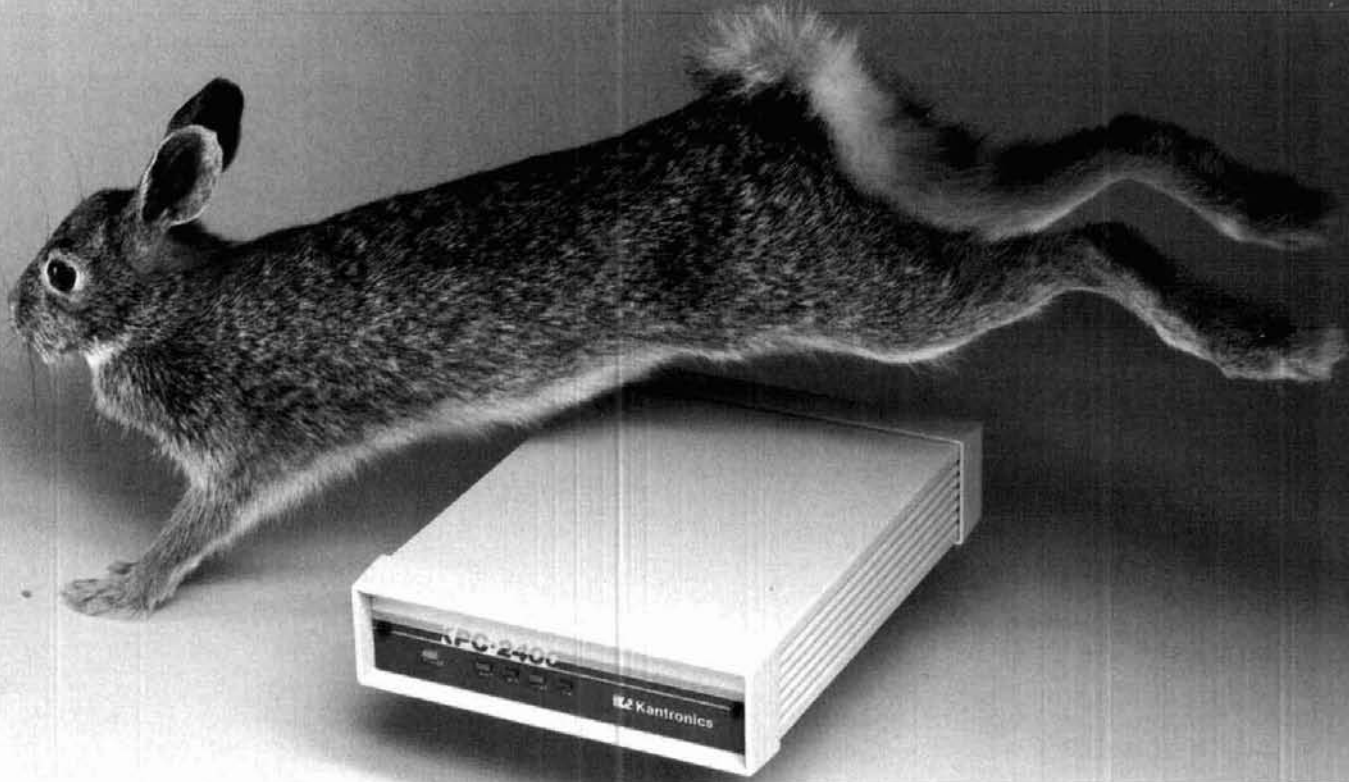
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FORMATTED DISPLAY OF PACKETS USING KISS

By Michael Pechura, WA8BXN, CIS Department, Cleveland State University, E. 24th at Euclid Avenue, Cleveland, Ohio 44115

Format your packets for readable display

In the October issue, I talked about the basics of displaying the information found in individual packet radio packets using KISS mode. You'll recall that KISS sends raw packet frames from the TNC to a computer as a set of bytes, without interpreting the header or other content of the packets.

This month I'll look at packet format and how to display the various fields in a readable form. I'll also discuss BASIC programs that can be run on either a C-64 or an IBM PC computer.

Each packet consists of two major portions: the header and the data (which may be absent). When operating in KISS mode, the TNC sends a packet to the computer by starting with a byte that is **C0** in hex, followed by a byte that is usually zero. This is followed by all the bytes of a packet and finally ends with another byte of hex **C0**.

The TNC makes the following replacements to avoid problems with packets that themselves contain bytes of hex **C0**. A byte of hex **C0** found in a packet to be sent to the computer is replaced by 2 bytes, **DB DC**. A byte of hex **DB** found in a packet is replaced by **DB DD**. This solves the transparency problem. When the computer receives either of these byte pairs from the TNC, it must replace them with the corresponding single byte to get the actual packet content.

For example, if a packet actually contained the data bytes **DA DB DC DD** the computer would receive the following from the TNC: **DA DB DD DC DD**.

As I've already mentioned, a packet contains two major parts: the header and the data portion. For some packets, the data portion isn't used. Within the header there are also two parts: the address and the command byte. The address contains the calls of the sending and receiving stations as well as the calls of any digipeaters used. The command byte tells what kind of packet it is along with sequence number information for some types. The relation of these fields is shown below:

Packet			
Header		Data	
Address bytes	Command Byte	PID	Data Bytes

The address bytes consist of two or more fields, each 7 bytes long. The first two fields give the destination and origination callsign, respectively. Call these the "tocall" and "fromcall." Any additional fields give digipeater callsigns (the "VIA" list). Thus for the address bytes we have:

Address bytes			
tocall	fromcall	digicall	digicall

Within each of these callsign fields, the first 6 bytes give the callsign. The last byte gives, among other things, the - ## (WA8BXN-01) often found after calls. This byte is called the Secondary Station ID (SSID). These callsign fields can't be printed as ASCII characters as they are found in a packet, because some encoding is done.

The first 6 bytes of each callsign field containing the callsign are each shifted left 1 bit position, making the right bit of each byte equal to zero. If the callsign has less than 6 characters, blanks (also shifted left one bit position) are added on the right to make a total of 6 bytes. The SSID byte also has the SSID number shifted left 1 bit. All these bytes are shifted left one bit position to make room for the bit that indicates the end of the

address bytes. All but the rightmost address byte will have a zero bit in its rightmost bit position. The rightmost address byte has a one bit in its rightmost bit position signaling the end of the address bytes.

Callsign field in address	
6-byte callsign shifted left one bit	SSID byte

The use of the bits in the SSID byte depend on which callsign it's associated with -- the to/from calls or digipeater calls. In both cases the SSID number bits are found in the same place:

Bit Positions							
7	6	5	4	3	2	1	0
SSID number							0

Because the SSID number is a 4-bit number, it can have values of 0 through 15. Callsigns with an SSID number of zero generally don't show the -0. The rightmost bit of the SSID byte is zero for all SSID bytes (and callsign bytes) except for the last one. Thus the end of the address field of a packet is indicated by a one bit in the rightmost bit of an SSID byte. Bits 5 to 7 of an SSID byte have different meanings. For example, bit 7 in the SSID byte is used with digipeater calls. When set to 1 it means that a digipeater has repeated the packet.

The "tocall" of WA8BXN-3 is an example of a callsign field. The hex for the ASCII representation of WA8BXN is **57 41 38 42 58 4E**. Each of these bytes must be shifted left one bit position. Because the ASCII coding of characters uses only 7 bits, no information is lost by this left shift. The W (01010111 in binary) becomes hex **AE** (10101110 in binary). The SSID number (3) in binary is 0011. Thus we have:

W	A	8	B	X	N	-3	Original callsign
AE	82	70	84	B0	9C	06	Encoded callsign

If this had been the last callsign in the address, the SSID byte would have been **07**. If this was the digipeater call of a digipeater that repeated this packet, the SSID byte would be **86** (or **87** if it was the last digipeater).

There are three basic kinds of command bytes for the three kinds of packets. The rightmost 1 or 2 bits of the command byte indicate the type of packet:

Command Byte								
							0	Information frame
							0 1	Supervisory frame
							1 1	Unnumbered frame

The use of the remaining bits in the command byte depends on the packet type. In the case of an Infor-

mation frame (I), there are two sequence numbers and a Poll bit. The sequence numbers are N(S), the sequence number of this frame, and N(R), the sequence number of the next I frame expected in reply. The sequence numbers take on values of 0 through 7 and then repeat. Use of the Poll bit varies; its value will be displayed later.

N(R)	Poll	N(S)	0	Information frame
------	------	------	---	-------------------

There are three kinds of Supervisory frames; all are used to acknowledge receipt of I frames. Each contains an N(R) sequence number; i.e., the sequence number N(S) expected in the next I frame received. This acknowledges reception of all lower numbered I frames. A Poll/Final bit is also found in the command byte. It, too, will be displayed later.

N(R)	P/F	0	0	0	1	Receive Ready (RR)
N(R)	P/F	0	1	0	1	Receive Not Ready (RNR)
N(R)	P/F	1	0	0	1	Reject (REJ)

The final command type (Unnumbered) has the most variations. The majority of them have to do with connecting and disconnecting. This group also contains beacon transmission information. In each command byte of this group the rightmost 2 bits are both 1s, indicating that it's a U frame. Five bits are used to specify the particular command. They are split into groups of 3 bits and 2 bits with a Poll and/or Final bit in between them.

0	0	0	P/F	0	0	1	1	Unnumbered Information
0	0	0	F	1	1	1	1	Disconnected Mode
0	0	1	P	1	1	1	1	Set Async Balanced Mode
0	1	0	P	0	0	1	1	Disconnect
0	1	1	F	0	0	1	1	Unnumbered Acknowledge
1	0	0	F	0	1	1	1	Frame Reject

With 5 bits to specify the particular function to be done, there could be as many as 32 different functions. Only the 6 given above are typically used in packet radio. Unnumbered Information frames contain data bytes following the command. These frames are often used for beacons and are sent when a TNC is used in Converse mode, while not connected to another station.

Some of these commands are often used in pairs. For example, to establish a connection the Set Asynchronous Balanced Mode (SABM) command is sent. The expected reply to this is Unnumbered Acknowledge (UA). If the station to which the SABM is sent doesn't wish to enter into a connection, the reply will be Disconnected Mode (DM). This usually causes a "Busy" message to be displayed.

Disconnect (DISC) is sent to terminate a connection. The reply to this is normally UA.

The last of the Unnumbered frame types is Frame Reject (FRMR). This packet type is sent when an error is detected that can't be corrected by simply resending an improperly received frame. Three data bytes that try to indicate what went wrong follow the command byte.

The last packet field requiring some explanation, contains the data bytes. Data bytes are found only in I frames and UI frames. The data field contains a Protocol Identifier (PID) byte followed by zero or more actual data bytes. Normally the PID is F0 in hex. Other PID values may be used by some variations of the standard protocol. A PID of hex CF is used between NET/ROMS nodes, for example.

This short explanation of the fields found in packets gives the basic information you need to understand what the program displays. A more complete description of the AX.25 protocol is found in the book *AX.25 Amateur Packet-Radio Link-Layer Protocol*, published by the ARRL. This book discusses how these fields are used and the way they inter-relate to each other, along with details on their format.

The program presented in this article gives you another way to understand how all these formats and commands fit together. It lets you watch the packets in action, with all the fields displayed in a readable fashion. The only thing you can't see are the CRC bytes in the packets. These are checked by the TNC and not made available to the computer.

I've provided two versions of the program — one for the IBM PC (and clones) in fig. 1 and one for the C-64 in fig. 2. Both are very similar so the program discussion applies to either. They've been written for use with a Kantronics TNC that has been set up for operation at 600 baud between the TNC and computer.

I minimized the program comments in the interest of increased speed and reduced typing. The program can be divided into the following sections:

Lines	Purpose
20 — 30	Initialize serial port and screen colors. In IBM PC version, substitute COM1 or COM2 where appropriate.
40	Put TNC in KISS Mode. Modify or delete as needed for non-Kantronics TNCs.
50	Wait for beginning of frame (hex C0 = 192 decimal).
60	Get & ignore 0 byte, print separator line.
70	Clear string TXT\$ (will be used in later addition).
80	Get & print tocall < ---from call.
90 — 120	Get & print digipeater list.
140	Get command byte.
150	If other than I frame continue at 270.
160 — 170	Display I frame command fields.

180	Get & display PID byte in hex.
190	Get & test next byte. If hex C0 it's end of frame, so go back to 50 to wait for next packet.
200 — 250	If data byte is printable, print as character. If not, then line 250 displays it in Hex in a different color. The C-64 version swaps capital and lower case letter codes to make them appear right on the screen.
280 — 330	If it's a Supervisory frame, print fields of command then continue at line 190 to print any data found (there shouldn't be any).
350 — 430	Display Unnumbered frame's command name and P/F bit. If frame is UI frame, go to line 180 to show PID and data. Otherwise go to line 190 to read hex C0 byte that ends frame.
450 — 490	Subroutine to read 6 bytes of callsign (shifting each right 1 bit by dividing by 2) and print them. SSID number is extracted from 7th byte read and printed if not zero.
500 — 550	Wait for byte to arrive from TNC then read it. If it's one of the special pairs (DB DC or DB DD) return the single byte for which they appear.
560	Print the number in A as two hex characters.

After typing the appropriate version of the program into the computer, be sure to save it before you proceed. If you find and correct any syntax errors, save the program again before running. Before running the program make sure the TNC is set up for 600 baud operation to the computer.

The following is representative of what you should see as output from the program. The actual number of characters per line seen on the screen will be different from the lines lengths used here. Those data bytes that aren't printable as characters are represented instead as two hex digits, displayed in a different color from other data bytes.

```
-----
WA8XXX < --K8XXX: UNNUMBERED FRAME
UNNUMBERED ACKNOWLEDGE F = 0
-----
WA8XXX < --K8XXX: SUPERVISORY
FRAME N(RCV) = 1 P/F = 0 RECEIVE READY
-----
BEACON < --AX6X: UNNUMBERED FRAME
UNNUMBERED INFORMATION P/F = 0 PID = F0
: AX6X HIGHLAND HTS — BBS AX6X-20D
-----
W8XXX < --KX8XX: INFO FRAME N(RCV) = 0
P = 0 N(SENT) = 1 PID = CF: 9688p8
E86@ AEpA298B2@a@02FB000003
```

FIGURE 1

```

10 REM DISPLAY PACKETS USING KISS --- IBM PC VERSION (600 BAUD)
20 CLOSE 2:COLOR 7,0,0:CLS
30 OPEN "COM2:600,N,8,1,CS,DS,CD" AS 2:HS="0123456789ABCDEF"
40 PRINT#2,"KISS ON"+CHR$(13)+"RESET"
50 GOSUB 500:IF A<>192 THEN 50
60 GOSUB 500:PRINT "-----"
70 TXT$=""
80 GOSUB 450:PRINT " <--> ":GOSUB 450
90 IF (A AND 1)=1 THEN 120
100 PRINT "VIA ";
110 GOSUB 450:IF (A AND 1)=0 THEN PRINT ",,":GOTO 110
120 PRINT " ";
130 REM
140 GOSUB 500:REM GET COMMAND BYTE
150 IF A AND 1 THEN 270 ELSE REM ITS AN INFORMATION FRAME
160 P=(A AND 16)/16:PRINT "INFO FRAME N(RCV)=";INT(A/32);" P=";P;
170 PRINT " N(SENT)=";(A AND 14)/2;
180 GOSUB 500:PID=A:PRINT " PID=";:GOSUB 560:PRINT " ";
190 GOSUB 500:IF A=192 THEN PRINT:GOTO 50
200 IF PID=207 THEN TXT$=TXT$+A$
210 IF A<32 OR A>126 THEN 250
220 IF A>=65 AND A<=90 THEN PRINT A$;:GOTO 190
230 IF A>=97 AND A<=122 THEN PRINT CHR$(A AND 223);:GOTO 190
240 PRINT A$;:GOTO 190
250 COLOR 1:GOSUB 560:COLOR 7:GOTO 190
260 REM
270 IF A AND 2 THEN 350 ELSE REM ITS A SUPERVISORY FRAME
280 PRINT "SUPERVISORY FRAME N(RCV)=";INT(A/32);"P/F=";P;
290 SS=(A AND 12)/4
300 IF SS=0 THEN PRINT " RECEIVE READY";
310 IF SS=2 THEN PRINT " RECEIVE NOT READY";
320 IF SS=3 THEN PRINT " REJECT";
330 GOTO 190
340 REM
350 PRINT "UNNUMBERED FRAME ";B=(A AND 12)/4+(A AND 224)/8
360 IF B=7 THEN PRINT "CONNECT REQUEST P=";
370 IF B=8 THEN PRINT "DISCONNECT REQUEST P=";
380 IF B=3 THEN PRINT "DISCONNECTED MODE F=";
390 IF B=12 THEN PRINT "UNNUMBERED ACKNOWLEDGE F=";
400 IF B=17 THEN PRINT "FRAME REJECT F=";P;";
410 IF B THEN PRINT P;:GOTO 190
420 PRINT "UNNUMBERED INFORMATION P/F=";P;:GOTO 180
430 PRINT "UNKNOWN TYPE ";:GOSUB 560:PRINT " P/F=";P;";:GOTO 190
440 REM
450 FOR I=1 TO 6:REM MAKE A CALLSIGN PRINTABLE
460 GOSUB 500:A=INT(A/2):IF A<>32 THEN PRINT CHR$(A);
470 NEXT I
480 GOSUB 500:B=(A AND 30)/2:IF B THEN PRINT -B;
490 RETURN
500 A$=INPUT$(1,2):REM GET BYTE FROM TNC
510 IF A$=""THEN A$=CHR$(0)
520 A=ASC(A$):IF A<>219 THEN RETURN
530 A$=INPUT$(1,2)
540 IF ASC(A$)=220 THEN A$=CHR$(192):A=192:RETURN
550 A$=CHR$(219):A=219:RETURN
560 PRINT MID$(HS,INT(A/16)+1,1)+MID$(HS,(A AND 15)+1,1):RETURN

```

IBM PC version.

KX8XX<--W8XXX: SUPERVISORY FRAME N(RCV) =
2 P/F = 0 RECEIVE READY

ID<--WB8XXX: UNNUMBERED FRAME
UNNUMBERED INFORMATION P/F = 0 PID =
F0: Network node (CLE)0D

KA8XXX-1<--WB8XXX: SUPERVISORY
FRAME N(RCV) = 1 P/F = 0 RECEIVE READY

BEACON<--KX3X VIA K3XXX: UNNUMBERED FRAME
UNNUMBERED INFORMATION P/F = 0 PID = F0:
Mail for: NWPAWX ALL DX KX3X NETROM N3XXX
VE3XXX0D

WA8XXX<--K8XXX: INFO FRAME N(RCV) = 1 P =
0 N(SENT) = 1 PID = F0: ok0D

WA8XXX<--K8XXX: UNNUMBERED FRAME
DISCONNECT REQUEST P = 0

NX8X<K8XXX: UNNUMBERED FRAME CONNECT
REQUEST P = 0

WA8XXX<--K8XXX: INFO FRAME N(RCV) = 3
P = 0 N(SENT) = 0 PID = F0: ka = po of10D

FIGURE 2

```

10 REM DISPLAY PACKETS USING KISS --- C-64 VERSION (600 BAUD)
20 CLOSE 2:PRINT CHR$(147)+CHR$(5)+CHR$(14)::POKE 53280,
0:POKE 53281,0
30 OPEN 2,2,3,CHR$(7):HS="0123456789ABCDEF":GET#2,A$
40 PRINT#2,"KISS ON"+CHR$(13)+"RESET"
50 GOSUB 500:IF A<>192 THEN 50
60 GOSUB 500:PRINT "-----"
70 TXT$=""
80 GOSUB 450:PRINT " <--> ":GOSUB 450
90 IF (A AND 1)=1 THEN 120
100 PRINT "VIA ";
110 GOSUB 450:IF (A AND 1)=0 THEN PRINT ",,":GOTO 110
120 PRINT " ";
130 REM
140 GOSUB 500:REM GET COMMAND BYTE
150 IF A AND 1 THEN 270 ELSE REM ITS AN INFORMATION FRAME
160 P=(A AND 16)/16:PRINT "INFO FRAME N(RCV)=";INT(A/32);" P=";P;
170 PRINT " N(SENT)=";(A AND 14)/2;
180 GOSUB 500:PID=A:PRINT " PID=";:GOSUB 560:PRINT " ";
190 GOSUB 500:IF A=192 THEN PRINT:GOTO 50
200 IF PID=207 THEN TXT$=TXT$+A$
210 IF A<32 OR A>126 THEN 250
220 IF A>=65 AND A<=90 THEN PRINT CHR$(A OR 32)::GOTO 190
230 IF A>=97 AND A<=122 THEN PRINT CHR$(A AND 223)::GOTO 190
240 PRINT A$;:GOTO 190
250 PRINT CHR$(158);:GOSUB 560:PRINT CHR$(5);:GOTO 190
260 REM
270 IF A AND 2 THEN 350 ELSE REM ITS A SUPERVISORY FRAME
280 PRINT "SUPERVISORY FRAME N(RCV)=";INT(A/32);"P/F=";P;
290 SS=(A AND 12)/4
300 IF SS=0 THEN PRINT " RECEIVE READY";
310 IF SS=2 THEN PRINT " RECEIVE NOT READY";
320 IF SS=3 THEN PRINT " REJECT";
330 GOTO 190
340 REM
350 PRINT "UNNUMBERED FRAME ";B=(A AND 12)/4+(A AND 224)/8
360 IF B=7 THEN PRINT "CONNECT REQUEST P=";
370 IF B=8 THEN PRINT "DISCONNECT REQUEST P=";
380 IF B=3 THEN PRINT "DISCONNECTED MODE F=";
390 IF B=12 THEN PRINT "UNNUMBERED ACKNOWLEDGE F=";
400 IF B=17 THEN PRINT "FRAME REJECT F=";P;";
410 IF B THEN PRINT P;:GOTO 190
420 PRINT "UNNUMBERED INFORMATION P/F=";P;:GOTO 180
430 PRINT "UNKNOWN TYPE ";:GOSUB 560:PRINT " P/F=";P;";:GOTO 190
440 REM
450 FOR I=1 TO 6:REM MAKE A CALLSIGN PRINTABLE
460 GOSUB 500:A=INT(A/2):IF A<>32 THEN PRINT CHR$(A);
470 NEXT I
480 GOSUB 500:B=(A AND 30)/2:IF B THEN PRINT -B;
490 RETURN
500 IF PEEK(667)=PEEK(668) THEN 500:REM GET BYTE FROM TNC
510 GET#2,AS:IF A$=""THEN A$=CHR$(0)
520 A=ASC(AS):IF A<>219 THEN RETURN
530 IF PEEK(667)=PEEK(668) THEN 530
540 GET# 2,AS:IF ASC(AS)=220 THEN AS=CHR$(192):A=192:RETURN
550 AS=CHR$(219):A=219:RETURN
560 PRINT MID$(HS,INT(A/16)+1,1)+MID$(HS,(A AND 15)+1,1):RETURN

```

C-64 version.

WA8XXX<--K8XXX: SUPERVISORY FRAME
N(RCV) = 4 P/F = 0 RECEIVE READY

WA8XXX<--K8XXX: UNNUMBERED FRAME
DISCONNECT REQUEST P = 0

Most of this information can be displayed using the monitor commands found in most current TNCs, without your having to do any programming. The point of this program isn't so much to provide a way to display such information, but rather to show how it can be done — and relate what's in a packet to what's displayed.

Many program modifications are possible. I strongly suggest that you run it without modification first. One of your initial additions to the program might be to put an asterisk after the call of the station that actually sent the packet (the one that was heard when digipeater calls are present in the header). Here's a chance to experiment, to build something new, without any additional expense other than time.

An unreduced copy of the program is available for an SASE. Ed.

Article F

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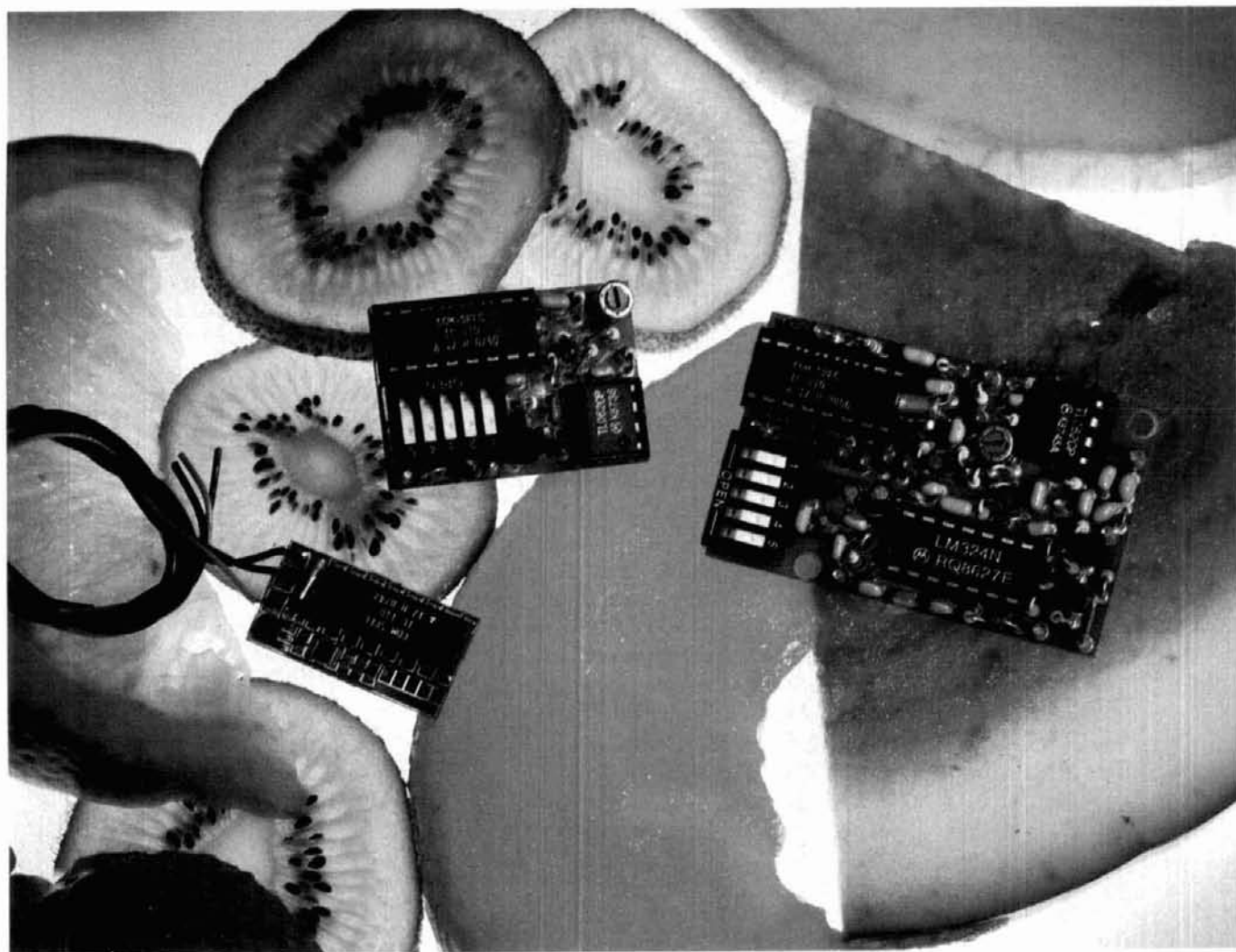
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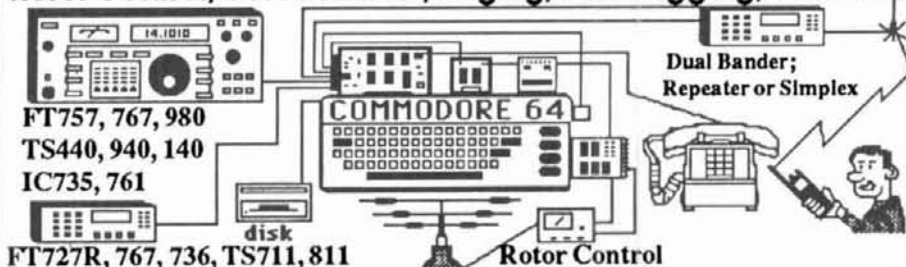
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AUTOPATCH REVERSE PATCH

- 1020** (18 digit) tele. #'s stored
- 300 users/CTCSS+ 2 tone page**
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- Directed/general/reverse page**
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- Security mode; T.Tone readback
- Reverse Patch active all modes**
- Call waiting/Quick dial/auto off
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- Dual VFO's/Rev/Split/COR
- Set Scan inc. & offset/resume
- Monitor mode & Link repeaters

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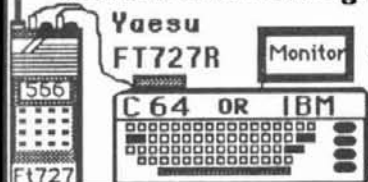
Model **CS64S \$349.95 + \$4.00** shipping USA; incl. pre-wired, tested computer interface, disk, cables & manual (simplex version on request)

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- Manual (Refunded).....**MN1 \$15.00**

MINI C.A.T. COMPUTER CONTROL FT-727R

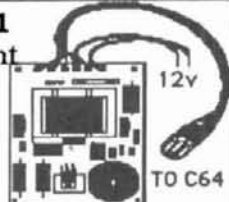
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- MODEL DCPS.....\$119.95**



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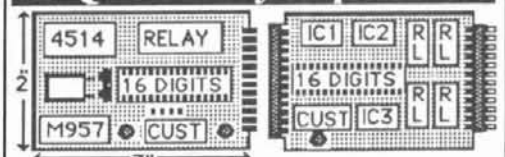
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product

REVIEW

Cushcraft R4 vertical antenna

The Cushcraft R4 vertical antenna is a newly designed version of the popular R3 model. Like the R3, the R4 is a half-wave no-radial design which covers 20, 15, and 10 meters. Unlike the R3, the R4 adds 12 meters to its frequency coverage, and eliminates motorized tuning in favor of a network which provides fully automatic frequency selection. Physically, the R4 is 18-feet long and approximately the same weight as its predecessor. (All hardware is stainless steel.) The R4 also looks different, sporting newer style traps, a capacitive hat, and 4-foot decoupling radials at the base. Maximum power rating is 1800 watts PEP.

Assembly

I found the R4 easy to assemble. Cushcraft's step-by-step instruction sheet was visual, showing the path of least resistance to final set-up without wasting a lot of words. For tools, I used a straight-blade screwdriver, a small wrench, and a steel measuring tape. The only assembly operation requiring patience was the decoupling radial bracket, a 4-piece affair held together by 12 screws. The rest of the job was easy. The most critical part of the antenna, a section lined with traps and stubs, comes fully pre-assembled from the factory. Only three simple measurements were needed during final assembly to "tune" the antenna.

Installation

The R4 is especially suited to places where installing a beam or horizontal dipole would be difficult or visually unacceptable. The antenna is very light in weight (8 lbs.), with only 1.4 square feet of wind-loading surface. Thus, I was able to mount mine on top of a 10-foot TV-mast pipe and clamp it to the chimney with Radio Shack® ratchet mounts. No guys were needed. When mounting on a small-diameter mast, check to make sure the end of the pipe doesn't extend past the mounting sleeve and up into the R4's fiber glass base insulator, since this will detune the antenna. Also, when connecting feedline, use the silicon sealer provided in the hardware pack. Without this, the aluminum UHF connector will eventually corrode, making it impossible to disconnect the coax! Finally, try to mount

the antenna up in the clear. The manual warns that close proximity to trees, buildings, feedlines, etc., will upset tuning and degrade performance.

Because the R4 is so easy to assemble and erect, I think it would make a great antenna for portable installations. It quickly breaks into two or three sections for transport, and the decoupling radials (four indestructible mobile-type whips) remove in seconds. Add a telescoping 18-foot mast, and you could be motor-home portable from almost any location!

Performance

The R4 is much simpler to use than the R3, since there are no remote-tuning adjustments to deal with. Band switching is fully automatic. You simply plug in the antenna, and operate.

I conducted my first on-air tests on 20 meters — the band most likely to show any compromise in performance. To keep things interesting, I used relatively low power (a Ten-tec Argosy, 50-watt PEP). I also placed a 20-meter dipole at 55 feet on-line for signal-strength comparisons. My prediction was that the 32-foot dipole would significantly outperform the 18-foot R4 — which had the additional handicap of being parked down between the trees on a single-story roof. However, I was in for a pleasant surprise! After several QSOs, I found both antennas generally performed within one S-unit of each other. While this in no way constitutes reliable "antenna range" testing, it did convince me that any compromise in the R4's performance due to its shorter length is minor, and possibly offset by a more favorable TOA.

Performance on the other bands was equally impressive. For example, I called CQ on a seemingly-dead 15-meter band, and was answered by F5GT, who gave me a 579 report. At noon, 10-meters yielded several good reports from South America.

Next, I ran SWR curves to see how closely this particular antenna, assembled on a picnic table and installed at my less-than-perfect location, matched those provided by Cushcraft. On all bands, I obtained readings of 1.2:1 or better at the point of resonance, with readings below 2:1 at the band edges. However, not all minimum SWR points landed where Cushcraft predicted they would — or in my favorite band segments. Although it will probably have little impact on actual performance, one day I plan to indulge my compulsion to tweak things just a bit closer.

Conclusion

Overall, I found the Cushcraft R4 easy to assemble and install. It's also easy to look at. For those reasons alone, I think it would make a great antenna for apartment, condo, motor-home, or portable use. But, beyond that, I was especially impressed with how well it worked. I think the R4 is a winner and I can recommend it.

K1BQT

DRSI PC*Packet Adapter and software

In twenty years, we'll look back at the '80s as the decade of the computer. Oh sure, they were available earlier, but they were more a curiosity and had limited capacity. Today there's a wealth of different machines available and you can pick and choose.

One of the most popular computer designs is the IBM PC and its various clones. Prices range from less than \$800 for a basic 8088 machine to — well the sky's the limit.

Another revolution has occurred in the Amateur field of digital communications. CW and RTTY have been around for years. But Packet Radio (computer to computer communications) has exploded and shows no sign of abating. It was only logical that, sooner or later, someone would mix the two technologies together and come up with a product that includes all the benefits and none of the limitations. One of the biggest complaints many packet users express is that when operating in packet mode, their machine could do nothing else. However, the PC Packet Adapter and controller software can be turned on and then run in a background mode, freeing you to do whatever else you want — without disconnecting from packet. This "running in the background mode" is what distinguishes the PCPA from other packet units.

DRSI's PC Packet Adapter is a plug-in, state-of-the-art, dual-port communications adapter card for the PC/clone computer. The PCPA has a 1200-baud modem for standard VHF/UHF packet operation. It connects directly to your radio through a DB-9 connector. The second port can be configured for either RS-232 or TTL level outputs. You can use the second port for either a HF modem or connection to a high-speed RF modem, among other possibilities.

The PCPA uses a 8530 serial communications controller running at just a hair under 5 MHz. It has flexible addressing and interrupt provisions. The "guts" of the PCPA include a complete 1200-baud modem on a single chip, controlled by the serial communications controller.

Installation is quick and simple. Disconnect all cables, open the computer, install the board, make up a cable to connect the radio to the TNC, put the computer back together and you're done. Total time — 15 minutes. The toughest part of the job is wiring the cables; DB-9s are awfully small for my big hands. (Pre-made cables are also available from DRSI.)

The key to the PCPA is the controller's software. The review unit arrived with version 1.0 software. DRSI has since released version 1.2. The program can handle up to 4 connections simultaneously using either version 1 or 2 AX.25 protocol. You'll be interested to know that the software can run both ports at the same time

(continued on page 70)

DECODING DATA SIGNALS

By James A. Sanford, WB4GCS, 20 Glen Forest Drive, Hampton, Virginia 23669

Algorithm improves teletype™ performance in noisy environment

Increasing numbers of Amateurs are involved in data communications. On VHF, many hams use fm transmitters to broadcast via Audio Frequency Shift Keying (AFSK). Direct FSK is the normal mode of transmission on hf.

In the absence of fm, hf data transmission is particularly sensitive to noise — especially at the higher data rates. Packet radio, even with its automatic error correction, is affected by high noise sensitivity. This results in frequent retransmission of packets, slowing the data transmission rate. Packet ensures the information will be correctly received *eventually*. I thought it was possible to do better and looked into ways to minimize this sensitivity.

hardware fixes

An obvious way to improve noise rejection is to modify the hardware used to convert audio signals into pulses for the computer or TTY. Line A of **fig. 1** shows the pulses transmitted to send the letter "R" in Baudot. **Figure 2** is a block diagram of a typical demodulator, similar to the ST-5 or the demodulator used in the PK-232. It consists of a limiter followed by a bandpass filter that removes all signals above and below the mark and space tones. A linear discriminator converts the frequency shift information to varying dc levels. The "slicer", a high-gain comparator, converts the discriminator output levels to discrete pulses which can be used to key a TTY or computer. The circuit is vulnerable to interference from spurious signals between the mark and space frequencies.

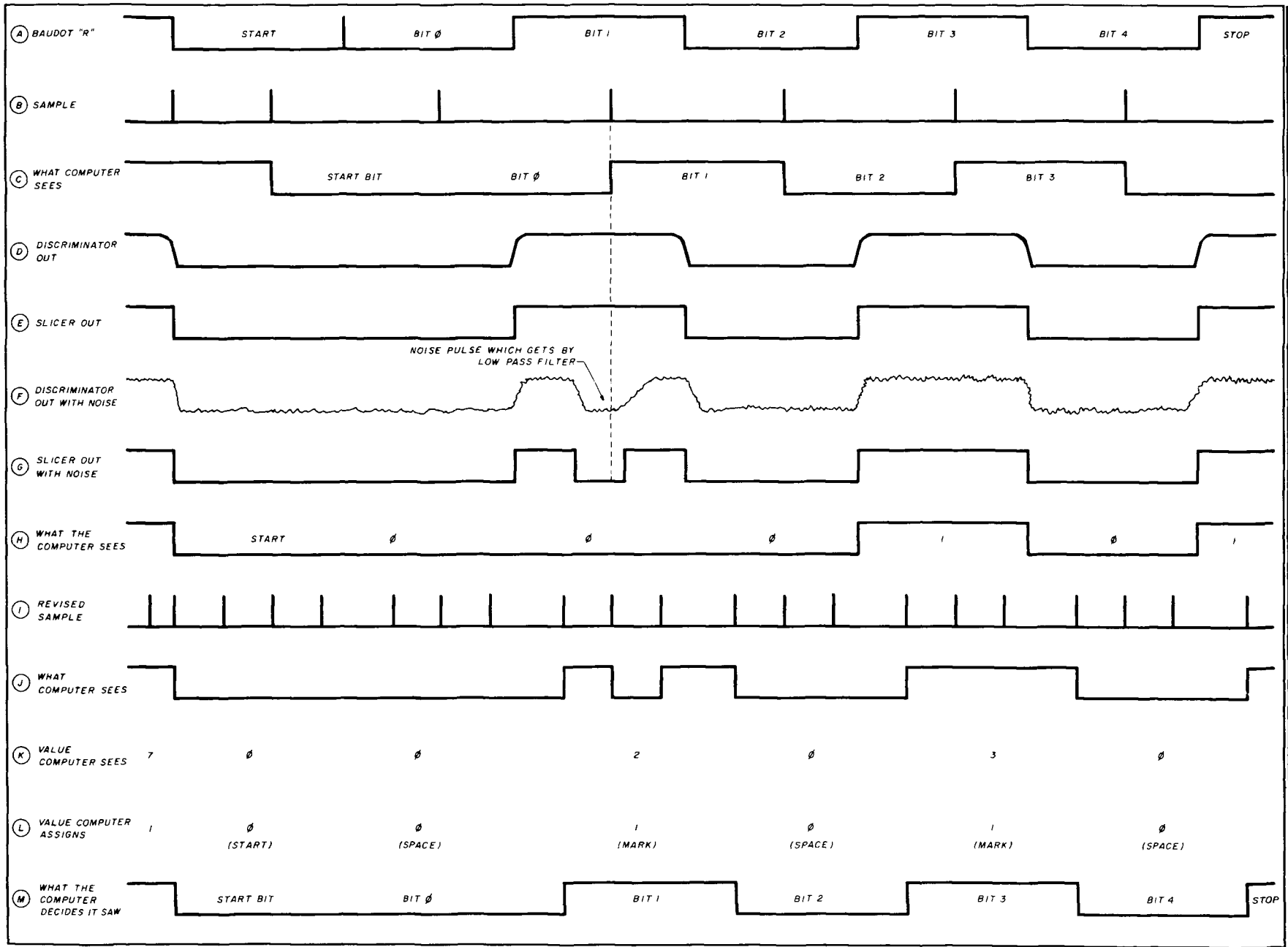
Figure 3 shows an improved demodulator. It uses separate filters to select the distinct mark and space frequencies, reducing the vulnerability to spurious signals

and improving the signal to noise ratio. Other hardware improvements are possible but difficult, so I turned to improving the computer.

software solutions

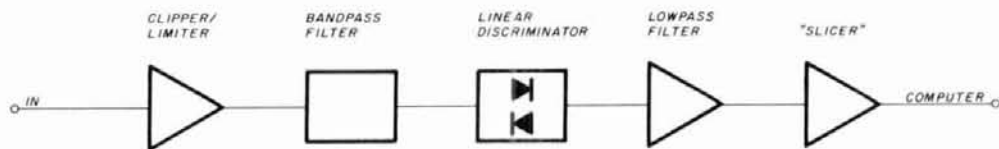
The flow chart in **fig. 4** shows how computer programs convert serial data to parallel information for storage and display. The input line is sampled at a rate that is a multiple of the bit rate. For this example, I've chosen a factor of 7. The computer samples the input for a start pulse. If one is present, the computer waits for one-half of the bit time and samples again. If the start bit is still there, the computer accepts this as a valid start pulse rather than noise. Delaying half a bit time puts the sample window near the center of each bit. The computer now delays a whole bit time and samples the input line for the first bit. After another full bit time delay, the computer gets the next bit. This continues until the last bit has been received and the entire character has been assembled. The character is now placed in a buffer to be stored, processed, or displayed. In **fig. 1**, line B shows the sample window. It is shown as a spike because it is so much shorter than the bit time (typically a few microseconds). Line C shows the data as the computer receives it — displaced by one-half bit time. The original pulse relationships and timing are maintained despite the delay. This sampling method resembles that used by hardware serial to parallel converters (ACIAs) like the 6551 and 6850.

In a noise-free system, the pulses emerging from the demodulator are identical to the original. In a noisy environment, the demodulator's discriminator contains noise which can corrupt the slicer's output (even though it's low-pass filtered). Line G of **fig. 1** shows the slicer output, and line H shows what the computer sees — an incorrect character which occurs because the computer looks at such a small window of the total bit time. A single noise pulse can corrupt the data, even though most of the bit is intact. Most Amateur systems waste time between samples; it is possible to use this time to make the computer smarter.



Waveform renditions of the letter "R" at various system locations.

FIGURE 2



Typical RTTY demodulator.

FIGURE 3



Improved RTTY demodulator.

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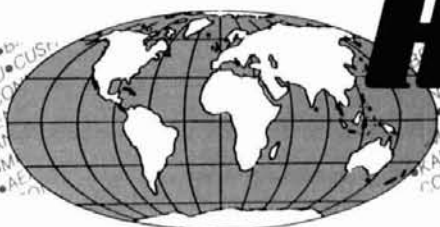
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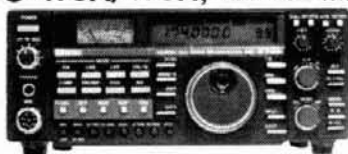
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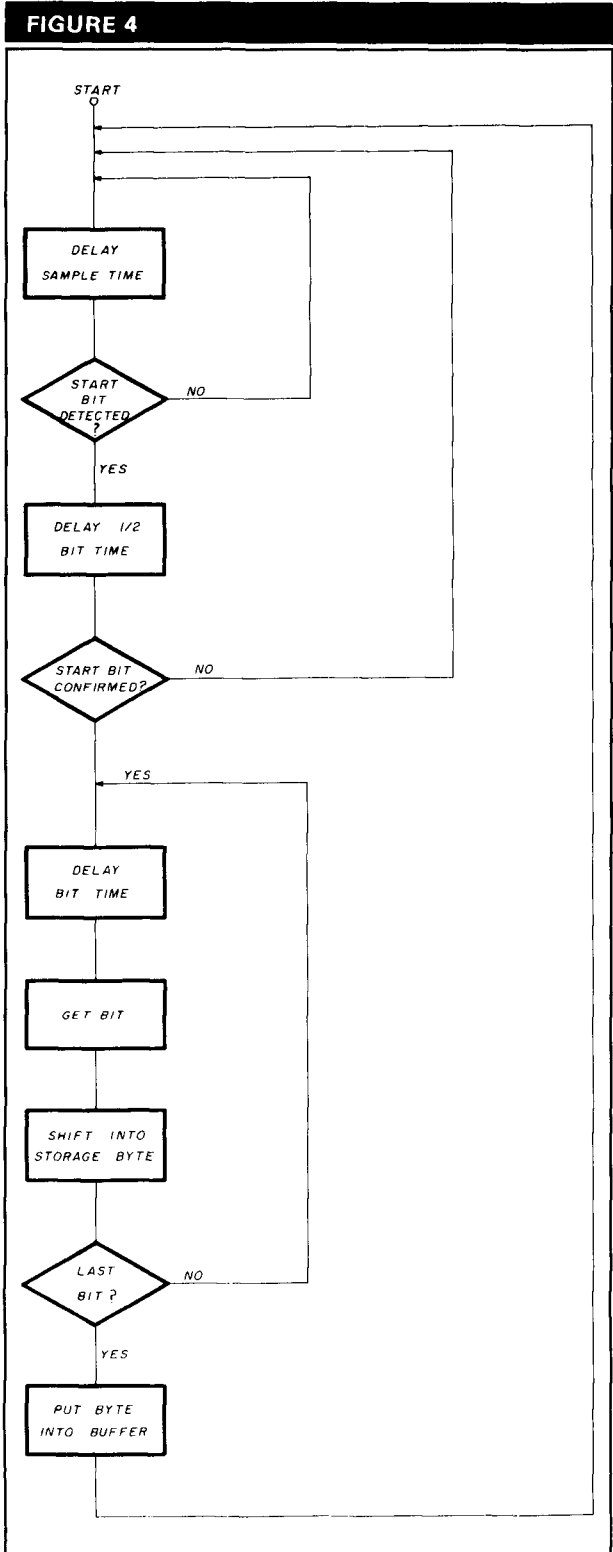
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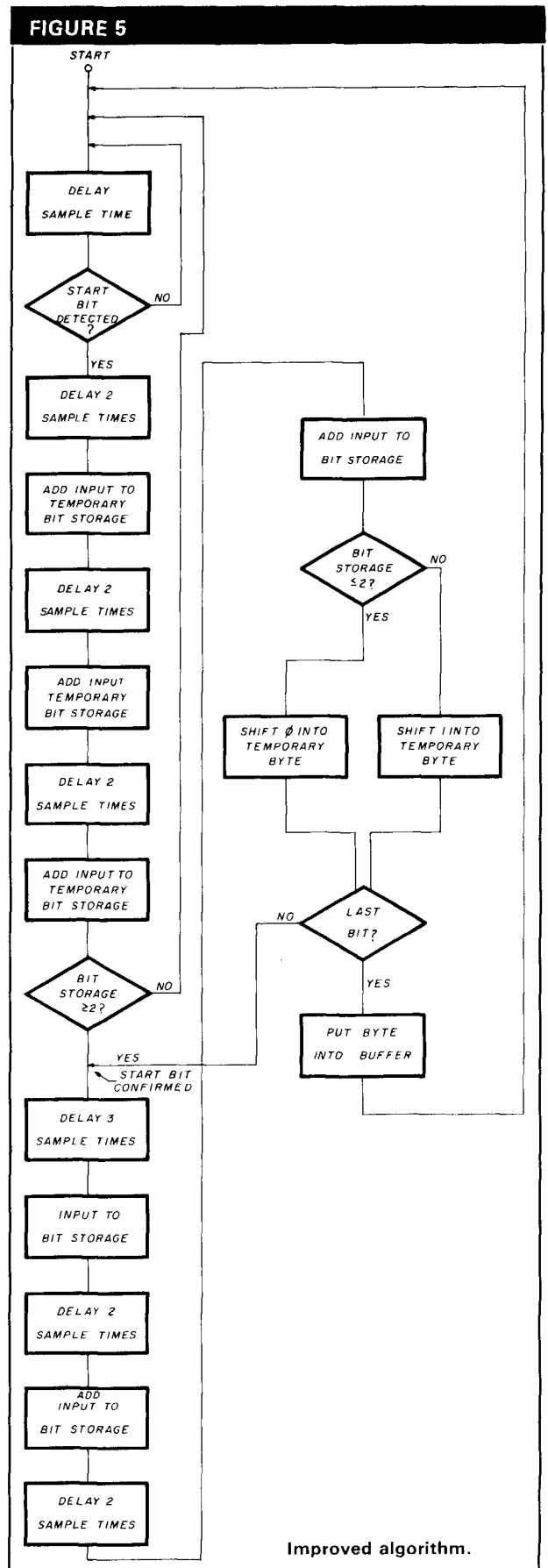
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Figure 5 shows a flow chart for an improved algorithm. Initially, the computer takes seven samples per bit time, looking for a start pulse. When it detects a possible start bit, the computer waits two sample periods and takes another sample. (The delay prevents



Serial to parallel decoding algorithm.



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FIGURE 6

```

00100 *****
00115 *SMART DEMODULATION ALGORITHM *
00125 *THIS INTERRUPT ROUTINE IS DESIGNED *
00135 * TO BE CALLED 21 TIMES PER BIT TIME *
00145 * IT ASSEMBLES THE RECEIVED CHARACTER *
00155 * AND STORES IT IN A BUFFER. BETWEEN *
00165 *INTERRUPTS, THE MAIN PROGRAM CAN GET *
00175 *THE CHARACTER AND DISPLAY IT. NOTE *
00185 * THAT A BAUDOT CHARACTER WILL BE *
00195 *AS SENT, AND LEFT JUSTIFIED. THE MAN *
00205 *PROGRAM MUST SHIFT THE CHARACTER INTO *
00206 *THE LSB'S AND TRANSLATE TO ASCII FOR *
00207 *STORAGE. (USE A TRANSLATION TABLE.) *
00208 *COPYRIGHT 1987 BY JAMES A. SANFORD *
00209 * WB4GCS/NNNOHF *
00210 *****
00220
00221 *WRITTEN IN 6809 ASSEMBLY LANGUAGE *
00222 *INCOMING DATA RECEIVED AT $FF22, BIT 0*
00250
00300 SZIN EQU $100
00310 SZOUT EQU $100
00360 BITS RMB 1 BITS/WORD INCLUDING START&STOP
00380 RXCTR RMB 1 BITS RCVD
00381 RBTSTR RMB 1 STORAGE FOR ACCUMULATED BITS
00386 RHITS RMB 1 STORAGE FOR NUMBER OF SAMPLES
00390 TXCKS RMB 1 TIMES PULSE CHECKED
00400 RXCKS RMB 1 TIMES PULSE CHECKED
00450 XTMP RMB 1 TEMP STORAGE FOR TX CHAR
00460 RTMP RMB 1 TEMP STORAGE FOR RX CHAR
00470
00480 DNXTI RMB 2 PTR FOR NEXT CHAR INTO OUT BUFFER
00490 ONXTO RMB 2 PTR FOR NEXT CHAR FROM BUFFER TO SEND
00500 INXTI RMB 2 PTR FOR NEXT RCVD CHAR TO BE STORED
00510 INXTO RMB 2 PTR FOR NEXT RCVD CHAR TO BE SHOWN
00550
00551
02600 TITLE INTERRUPT HANDLER
02610 FIRQ PSHS B
03215 RFIHQ RMB 1 RXCTR SEE IF RECEIVING ALREADY
03220 BEQ RFDNST NO, GO LOOK FOR START BIT
03225 DEC RXCKS YES
03230 BEQ RUPDT
03235 LBRA RIDON
03240
03245 RFDNST
03250 TST RXCKS IF 0, LOOKING FOR FIRST HINT OF START BIT
03255 BEQ FSTR1
03260 DEC RXCKS ALREADY INTO IT; CHECK DELAY
03265 LBNE RIDON STILL WAITING
03270 LDB $FF22 GET IT
03275 RORB
03280 BCS RSTR2
03285 INC RBTSTR UPDATE COUNTER
03290 RSTR2 INC RHITS UPDATE NUMBER OF SAMPLES
03295 LDB LDB RHITS
03300 CMPB #6
03305 BEQ RSTR3
03310 LDB #2 NOT DONE, DELAY
03315 STB RXCKS
03320 LBRA RIDON
03325
03330 RSTR3 LDB RBTSTR
03335 CMPB #4
03340 BLO NOSTRT NOT GOOD ENOUGH, START OVER
03345 LDB #11 DELAY INTO NEXT FRAME
03350 STB RXCKS
03355 LDB BITS SETUP TO GET DATA
03360 SUBB #2 ADJUST, ALREADY HAVE START BIT
03365 STB RXCTR
03370 RSTR4 CLR RHITS
03375 CLR RBTSTR
03380 LBRA RIDON
03385 NOSTRT CLR RXCKS
03390 BRA RSTR4
03395
03400 FSTR1 LDB $FF22
03405 RORB
03410 BCS RIDON NO START BIT, EXIT
03415 LDB #5 START BIT, DELAY
03416 STB RXCKS
03417 BRA RIDON
03420
03435 RUPDT LDB $FF22 GET DATA BIT
03440 RORB SHIFT INTO CARRY
03445 BCC RUPD1 DATA BITS A 0
03450 INC RBTSTR DATA BITS A 1, COUNT IT
03455
03460 RUPD1 LDB #2

```

Assembly language decoding algorithm for the 6809 microprocessor.

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03465	STB	RXCRC	WAIT 2 SAMPLE TIMES, START AGAIN
03467	INC	RHITS	
03470	LDB	RHITS	
03475	CMPB	#6	6 SAMPLES YET?
03480	BNE	RIDON	NO, DONE FOR NOW
03485	LDB	RBTSTR	WE HAVE 6 SAMPLES, HOW MANY WERE 1?
03490	RUF02	CMPB	#4
03495 *			IF (4, THE CMP WILL CAUSE A
03500 *			BORROW, AND SET THE C BIT IN THE
03505 *			CONDITION CODE REGISTER. WE'LL CALL
03510	EXG	B,CC	THIS BIT A ZERO.
03515 *			IF) 4 ONES, C WILL BE CLEAR, AND
03520	EORB	#1	WE'LL CALL THE BIT A 1
03525 *			THE C BIT IS THE COMPLEMENT OF THE
03530	EXG	B,CC	REAL DATA, SO TOGGLE THAT BIT
03535	LDB	RTMP	NOW RESTORE REGISTERS
03540	RORB		GET THE BITS WE'VE ALREADY GOT
03545	STB	RTMP	ROTATE NEW DATA BIT INTO TEMP
03550	LDB	#11	STORAGE
03555	STB	RXCRC	SETUP TODELAY 3 SAMPLES FOR NEXT BIT
03560	CLR	RHITS	
03565	CLR	RBTSTR	INITIALIZE COUNTERS
03566	DEC	RXCTR	
03570	BNE	RIDON	WE'RE DONE.
03650	RSTOR	PSHS	X
03660	LDB	INXTI	GET PTR
03670	LDB	RTMP	
03680	CMPB	#FF	CK FOR ERRONEOUS END OF DATA FLAG
03690	BNE	RSTOR1	WHICH MAY HAVE BEEN CAUSED BY NOISE
03700	LDB	#FE	IF SO, CHANGE TO FE, WHICH WON'T AFFECT
03710 *			BAUDOT, AND WILL HAVE MINIMAL EFFECT
03720 *			ON ASCII TEXT. (NEVER INTENDED TO XFER
03730 *			BINARY FILES IN ASCII)
03740	RSTOR1	STB	,X+ TOBUFFER
03750	CMPX	#INBUF+SZIN	
03760	BNE	RBFUP	
03770	LDB	#INBUF	
03780			
03790	RBFUP	STX	INXTI UPDATE BUF PTR
03800	CMPX	INXT0	THIS EXTRA ATTENTION TO BUFFER
03810	BNE	RBFUP1	MANAGEMENT IS NECESSARY TO
03820	LEAX	I,X	PREVENT NOISE INDUCED ERRATIC
03830	CMPX	#INBUF+SZIN	
03840	BLO	RBFUP2	BEHAVIOR DURING DISK OPERATIONS
03850	LDB	#INBUF	OR BUFFER TRANSMISSION.
03860	RBFUP2	STX	INXT0
03870	RBFUP1	PULS	X
03880			
03890	RIDON	PULS	B
03900	RTI		

framing errors.) This pattern continues until three samples have been made. If two or three of the samples indicate that a start bit was present, a valid start is assumed. If not, the computer reverts to sampling each sample period in search of a start bit.

When a valid start bit is detected, the computer waits three sample periods and makes the first sample in the first bit. Three samples are taken per bit, with a delay of two periods between stored samples. After the samples for each bit have been collected, it is determined if the bit was a zero or a one. (I've chosen a simple majority of samples scheme; more sophisticated methods are possible.) This continues until all bits have been received and the character is stored in the buffer. Line I of fig. 1 shows the revised sampling process; line J shows what the computer sees, given the noisy signal shown in lines F and G. Line K shows how the sample results are interpreted, and line L shows the results of the majority of samples. Line M shows the correctly reconstructed pulse train. Obviously, this process is not perfect. A long noise pulse which corrupts several samples within a bit can still corrupt the entire character.

This generic process can be enhanced in several ways. More samples per bit time yield greater noise immunity. The upper limit is determined by the amount of other processing your machine needs to do between samples.

You may wish to sample five times per bit at each sample period instead of every other sample period.

Although I've demonstrated the concept using Baudot code, the data can be simple ASCII or any other serial format. As mentioned earlier, using this process in a packet or AMTOR system can improve throughput by reducing the number of error-related retransmissions.

implementation

How do you put this to use in your system? The timing involved is too fast and critical for interpreted languages like BASIC. I used assembly language for the 6809 microprocessor with 21 samples per bit. (See fig. 6.) A compiled language like C will probably work as well, depending on the speed of your machine and the efficiency of your compiler. While I don't have the test equipment to make quantitative comparisons, on-the-air tests show that the "smart" algorithm is a noticeable improvement over a more conventional scheme.

I'm interested in any results you get using this method, suggestions you may have for improving the technique, or other ways you've found to improve data copy.

NOTE: A complete working program for the Radio Shack® TRS80 color computer 3 is available from the author for \$15.00. It features split screen, auto capture buffer (SELCALL), and several Baudot speeds as well as 300 baud ASCII.

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REVIEW

(continued from page 59)

facilitating "Gateway" station operation — VHF to HF digipeating.

Version 1.2 of the controller software is greatly expanded and includes many of the features advanced packeteers are looking for. Significantly updated is the basic TNC controller. Also included is a Terminate and Stay Resident, TSR, driver and THS, a split screen full color terminal program. The TSR program allows you to run the TNC in the "background" while running other PC programs. TSR also has a user accessible programming interface should you want to customize the program. THS includes pop-up windows for menus and support functions, scroll buffer, ASCII file transfers, connect directory, message storage and printer support. A more complete description is beyond the scope of this review. Also included is Packet.Bat, which loads the AX.25 driver and then starts the terminal program.

Using the PCPA is fun, especially if you want to use your computer as more than just a TNC controller. I'm sure that as more people use the card, new and more powerful software will be written to run the PCPA. DRSI has done its homework and offers a very good way to get into packet. Price for the PCPA is \$139.95; the HF modem is \$79.95.

DRSI is also distributing AA4RE's Multi Connect Bulletin Board System. This package is fully compatible with "RLI/MBL" systems, but has the advantage of supporting multiple simultaneous user connections on the same frequency. It does this without using any extra software, like Desqview or DoubleDOS. The AA4RE BBS is included with the DRSI PC*Packet Adapter at no cost.

For more information contact: DRSI, 2065 Range Road, Clearwater, Florida 34625.

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The books retail in the United States for \$2.95 each, plus \$1.00 shipping and handling. To order, contact your Kantronics dealer, HAM RADIO's Bookstore, or the factory.

For more information contact, Kantronics, Inc., 1202 E. 23rd Street, Lawrence, Kansas 66046.

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Contact EEB for additional information at 800-368-3270 or 703-938-3350.

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New guide to technical specs available from Nema1

Nema1 Electronics International has published a revised edition of its Cable and Connector Selection Guide. The new 40-page guide offers detailed technical specifications on more than 1000 military and commercial products. Product listings include triaxial cable and connectors, RF coaxial and semi-rigid cable and connectors, and crimping tools. To obtain a copy, please contact Nema1 Electronics International, Inc., 12240 N.E. 14th Avenue, North Miami, Florida 33161 or call 800-522-2253 or FAX your request to 1-305-895-8178.

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Versatile CTCSS encoder-decoder

Communications Specialists introduces the TS-32P Programmable CTCSS Encoder-Decoder. It has all the features of the TS-32, but uses a new microcircuit for more tone versatility. The new IC-110 microcircuit in the TS-32P contains a 32-bit reprogrammable memory that allows specification of any 32-tone frequencies from 15.0 Hz to 255.0 Hz. The desired tone frequency can be called from the memory with a five-position DIP switch mounted on the TS-32P circuit board. Frequency accuracy is ± .01 Hz.

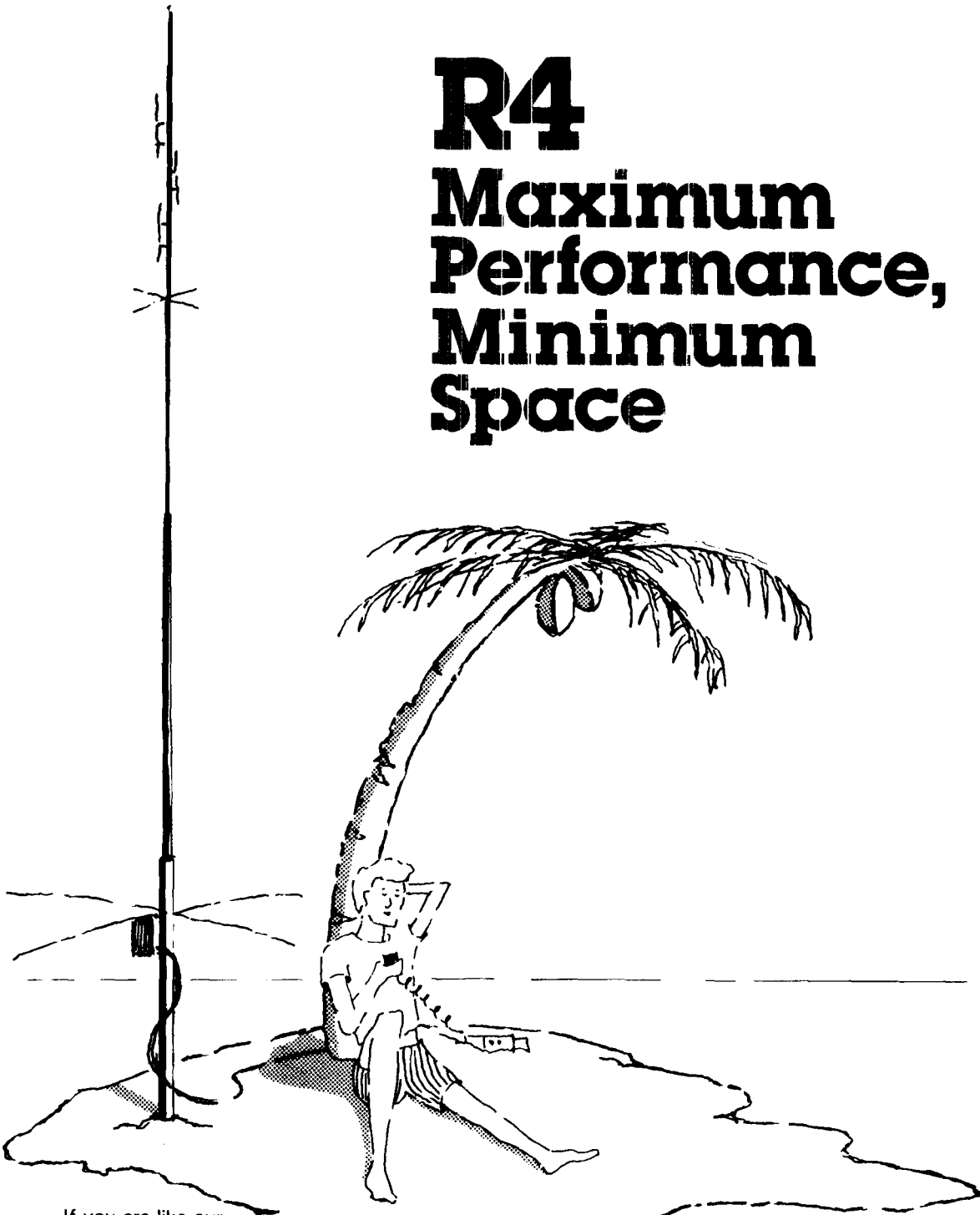
The TS-32P uses custom memory programming to provide multi-tone switching of up to six tones without requiring diode networks. The TS-32P allows easy access to any non-standard tone frequency. The 32-location tone memory can be changed with a handheld programmer available from Communications Specialists, or by returning it to the factory for re-programming at no charge.

The TS-32P measures 1.25" wide x 2.0" long x 0.40" high and operates on 6 to 25Vdc. The retail price of the TS-32P is \$57.95. A catalog is available on request.

(continued on page 104)

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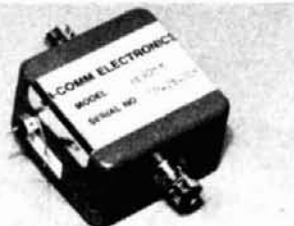
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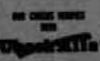
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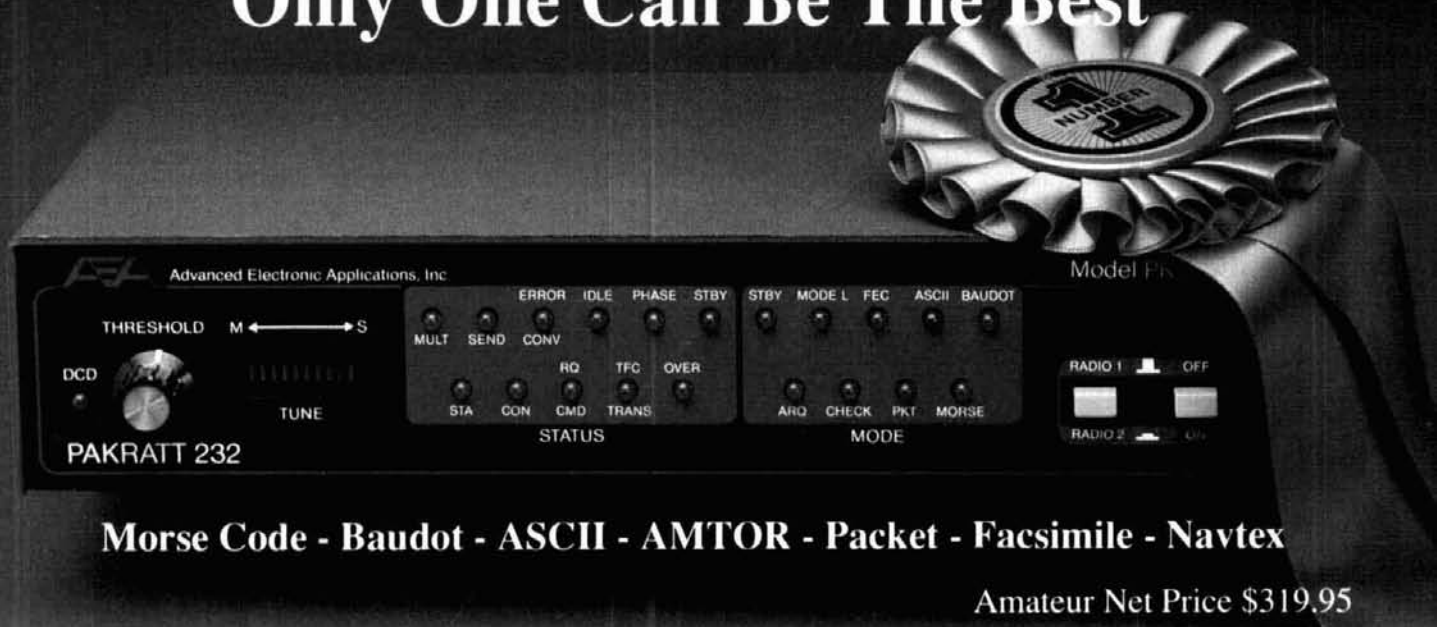
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A HOMEBREW TUNING DIAL

By John Pivnichny, N2DCH, 3824 Pembroke Lane, Vestal, New York 13850

Build a smooth, low cost, accurate dial for your next rig

Modern transceivers require precision tuning with zero backlash. This *analog* dial has 1-kHz markings and a 250-kHz tuning range. I used a commercial plastic circular disc protractor for the dial scale.¹ The dial can be constructed with home workshop tools. The information below can also be used to modify the dimensions, tuning ratio, tuning range, or tuning capacitor for your own homebrew equipment needs.

string drive

The dial's key feature is the use of dial cord and pulleys for the drive mechanism. Selecting the proper

pulley diameter makes almost any tuning ratio possible. For example, I wanted to use 250 degrees of dial rotation for a 0 to 250 kHz tuning range and 25 to 30 kHz per turn of the main knob to give a good tuning rate. This is about a 14:1 ratio.

I also wanted to use 160 degrees rotation of the tuning capacitor for this 250-kHz range. The capacitor shaft rotates 1.6 times slower than the dial shaft. A larger pulley provides the right ratio.

Calculations show that you need a 1/16-inch shaft for the main tuning knob, a 2-inch pulley for the dial shaft, and a 3-1/4 inch pulley for the capacitor shaft.

I used a variable capacitor, enclosed in a shield can with an oscillator coil, salvaged from the rear of an ARC5 Command set transmitter. Its ball bearing construction allows the shaft to rotate with very low friction. Most variable capacitors will work, but try to find one of these. Check with the old-timers at your local club or Fair Radio Sales.²

pulley construction

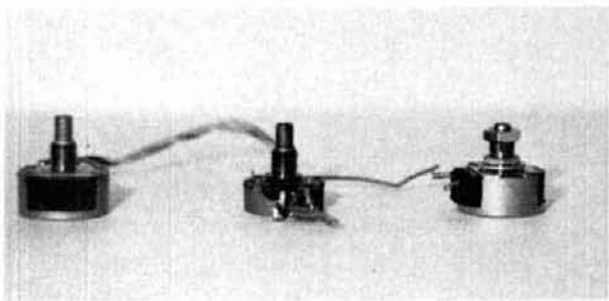
You'll have to make the pulleys, but this isn't hard. The raw material is Plexiglas™ sheets 3/16 or 1/4 inch thick available from glass supply shops. Pulleys with a diameter of 2-3/8 inch or less can be cut with the an electric drill hole cutter. The drill attachment (**fig. 1**) found in most hardware stores has a series of removable blades. (Another style is also shown.) Cut larger diameters with a jigsaw, coping, or saber saw.

After cutting the disc, remove any imperfections and cut the groove in the outer surface. Enlarge the center hole to 3/8 inch diameter. Find a potentiometer with a locking shaft (**fig. 2**). It looks like an ordinary potentiometer, but the mounting bearing has four or six slots and a one-way locking nut with a tapered diameter that can be tightened to secure the bearing to the shaft. You will also need five ordinary potentiometers. The resistance value doesn't matter because only the bearing will be used.³

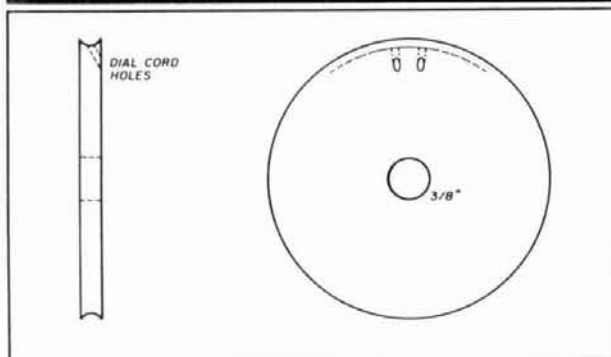
FIGURE 1



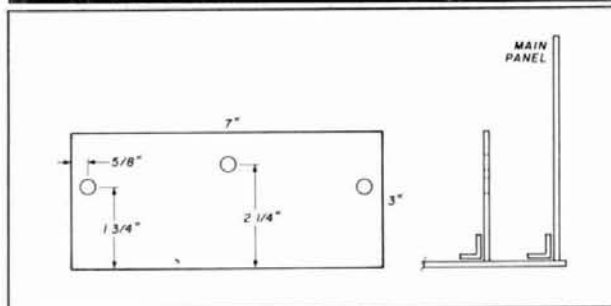
Drill attachments for cutting pulleys.

FIGURE 2

Potentiometer's source for bearings. Note one on right has a shaft-locking nut

FIGURE 3

Pulley details.

FIGURE 4

Mounting panel.

Gently extract the bearings from the potentiometers by removing a C-clip from the shaft and prying open the body. Tear away the top covers and discard the remains.

Purchase a 3-1/2 inch length of 1/4 inch steel shaft from the hardware store. You will need about 2 inches for the capacitor drive pulley and about 1-1/2 inches for the dial shaft pulley. Long shafts from the potentiometers can be salvaged and used. Mount a rough-cut pulley on the locking bearing, lock it onto the 1-1/2 inch shaft, and place it in the chuck of your electric drill. Clamp the drill body in a vise, turn it on with the locking button and start filing the outer edge.

When the pulley is perfectly round, use the edge

of the file to cut the groove. Drill small holes as shown (fig. 3) for the dial cord. This simple operation makes an excellent drive pulley.

panel mounting

Bearings, salvaged from the potentiometers, are fixed in a section of sheet aluminum mounted 1-1/16 inches behind the front panel. See fig. 4 for details. A 1 x 3 inch opening is cut in the main panel for the dial window. Two pieces of clear Plexiglas, 1/16 inch thick or less and 1-1/2 by 4 inches, are needed to cover the window opening and serve as a backup for the dial. Scribe a vertical line in the center of the front face on the rear Plexiglas piece. Fill the line with black ink to serve as a cursor. Use machine screws 4-40 x 3/4 inch to mount the Plexiglas parts to the front panel.

main drive shaft

A shaft 1/16 inch in diameter used with the main tuning knob drives the dial cord. Make this with brass rod, available at hobby shops. Cut 6-32 machine screw threads with a die as shown. Then thread on 1/4 inch spacers to fit the bearings and permit mounting the tuning knob. I used a 1-3/4 inch knob with two set screws.⁴

dial

Most of the circular protractors I have seen have two sets of numbers, one reading forward and one backward. I recommend you cut a circular disc of just the right diameter from Plexiglas to cover the inner set of numbers. Paint it an opaque color. I also filed a small notch for the 0 and 180 degree markings.

final assembly

The capacitor drive and dial pulleys are assembled as shown in figures 5A and 5B. Complete the assembly by mounting three bearings in the mounting bracket and one in the main panel. This one must be aligned with the shaft in place; first tighten the front bearing, then the rear one. You may need to use emery cloth on the shafts to insure smooth operation. Finally, string the dial cord as shown in fig. 6.

additional notes

I used the capacitor mentioned earlier by mounting it 5/8 inch off the bottom panel on two brackets.

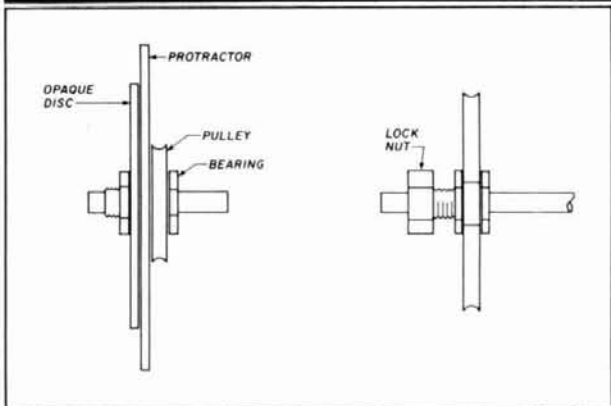
My favorite oscillator circuit is one that always works with any combination of L and C.⁵ Use silver mica capacitors in the tank circuit.

You can do some calculations to determine how far off a linear frequency dial will be with a linear capacitance tuning capacitor (see Appendix). In my case I wanted to tune 11.5 to 11.75 MHz. I calibrate the two ends of the dial, adjust L at the low frequency end and C at the high frequency end. The error at the center

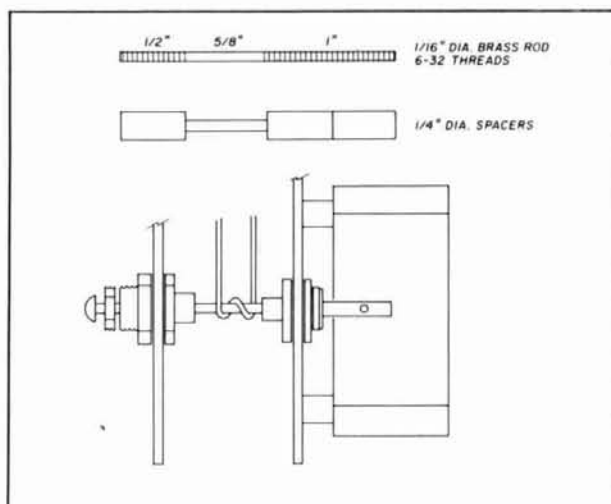
will be theoretically 2.0 kHz low. You can improve this by calibrating the ends 1 kHz high.

Because of the fairly large tuning capacitor I selected, I needed a very small inductor (about two turns on a 1/4 inch form). To allow for a more reasonable inductor, I modified the tank circuit to that shown in **fig. 8**. This reduces the effective capacitance by a factor of 4 and increases the allowable inductance by

FIGURE 5

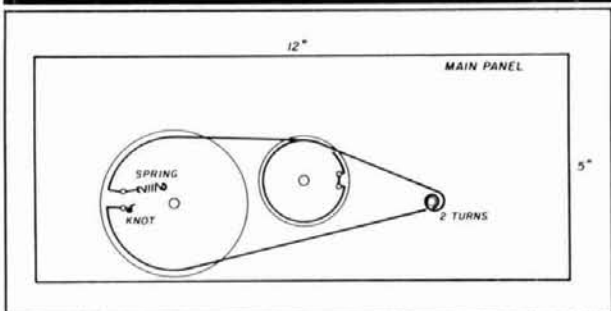


A. Pulley assembly.



B. Drive shaft.

FIGURE 6



Dial string diagram.

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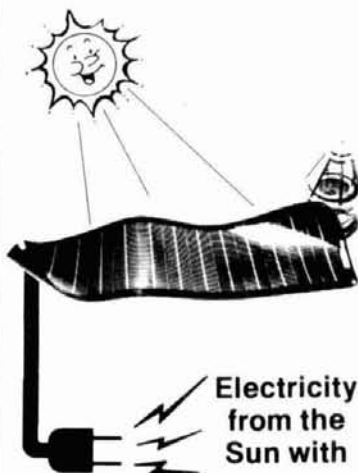
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that same factor. Note, however, that the theoretical error also increases to 4.7 kHz at the center of the dial.

measured results

Table 1 lists actual frequency counter readings taken with the circuits in figs. 7 and 8. The +2 to -3 kHz errors agree with the calculated figure of 4.7 worst case.

Resettability is excellent. Returning the dial to 0 degrees puts the output right back at 11,500. One turn of the main tuning knob covers 28 kHz.

There is no backlash or slippage, and because of

the high pulley ratio, no force is required to turn the knob. In these respects the dial is equivalent to an expensive zero backlash gear train drive like those used in modern transceivers.

Give this homebrew dial a try. I'm sure you'll enjoy its economy and accuracy.

references

1. Available at most stationery supply stores in the drawing instrument section.
2. Fair Radio Sales, Lima, Ohio.
3. Other sources of bearings are phone jacks and rotary switches.
4. The knob shown in the photograph is Electronic Hardware Corporation model EH71-4D skirted round Regent Series.
5. *Linear Data Book*, National Semiconductor, June 1976, pages 10-132.

Appendix

Assume you are using a linear capacitance variable which goes from C_{max} to C_{min} . (These values are not necessarily the maximum or minimum values but the ones used for the actual degrees of rotation.)

The low frequency will be:

$$F_{lo} = 1/2\pi \sqrt{L(C + C_{max})} \quad (1)$$

and the high frequency:

$$F_{hi} = 1/2\pi \sqrt{L(C + C_{min})} \quad (2)$$

These two equations (1) and (2) can be solved for the required fixed capacitance C.

$$(C + C_{max}) \times F_{lo}^2 = (C + C_{min}) \times F_{hi}^2 \quad (3)$$

$$C = \frac{C_{max} \times F_{lo}^2 - C_{min} \times F_{hi}^2}{F_{hi}^2 - F_{lo}^2}$$

Then at the center of the dial, the variable capacitor will be at:

$$(C_{max} - C_{min}) / 2 + C_{min} = (C_{max} + C_{min}) / 2 \quad (4)$$

and the frequency will be:

$$F_{mid} = 1/2\pi \sqrt{L[C + (C_{max} + C_{min}) / 2]} \quad (5)$$

In my case $C_{max} = 220$ pF, $C_{min} = 60$ pF, $F_{lo} = 11.5$ MHz, $F_{hi} = 11.75$ MHz.

$$C = \frac{220 \times 11.5^2 - 60 \times 11.75^2}{11.75^2 - 11.5^2} \quad (6)$$

$$C = 3580.43 \text{ pF}$$

From equation (1):

$$F_{lo} = k / \sqrt{3580.43 + 220} \quad (7)$$

At $F_{lo} = 11.5$, $k = 708.9477$ then:

$$F_{hi} = 708.9477 / \sqrt{3580.43 + 60} = 11.74999 \quad (8)$$

$$F_{mid} = 708.9477 / \sqrt{3580.43 + 140} = 11.62298$$

which for a correct dial should be 11.625 MHz, error = 2.0 kHz.

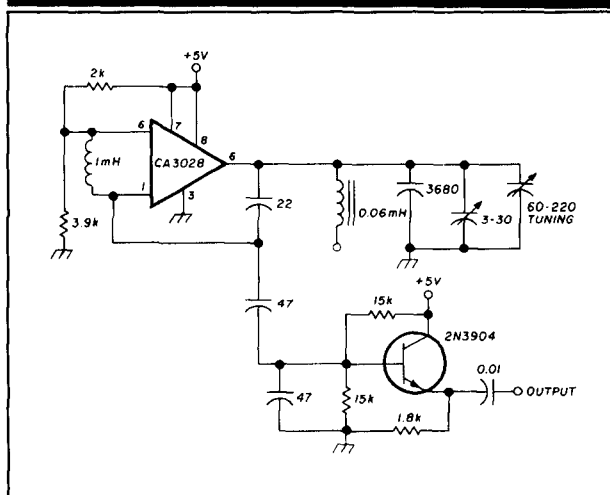
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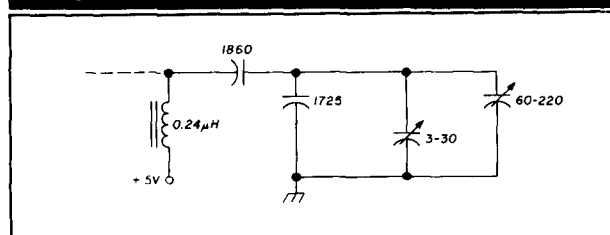
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FIGURE 7



Oscillator circuit.

FIGURE 8



Modified tank circuit.

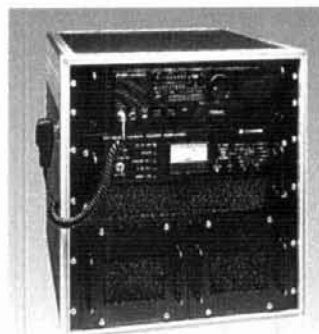
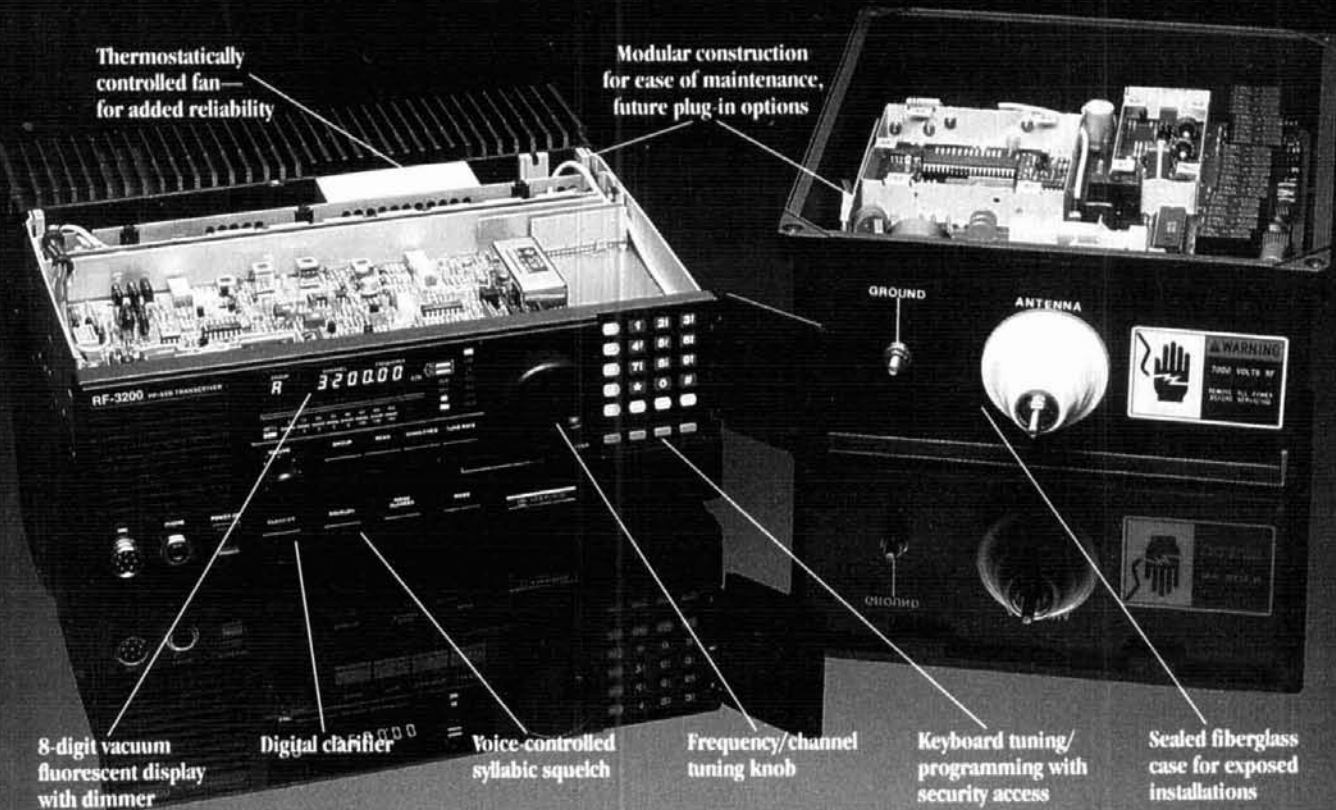
TABLE 1

Frequency counter readings taken with the oscillator and modified tank circuits.

dial setting (degrees)	frequency (kHz)	error (kHz)
0	11,500	0
50	11,549	-1
100	11,597	-3
150	11,647	-3
200	11,699	-1
250	11,752	+2

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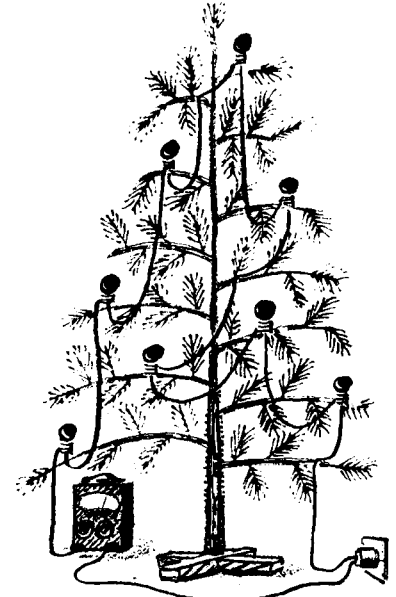
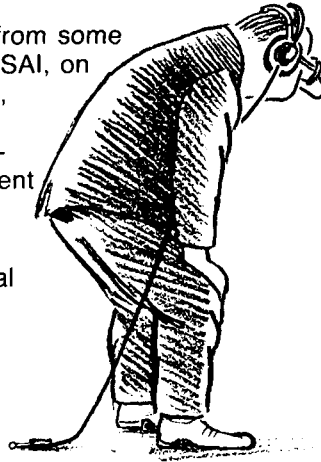
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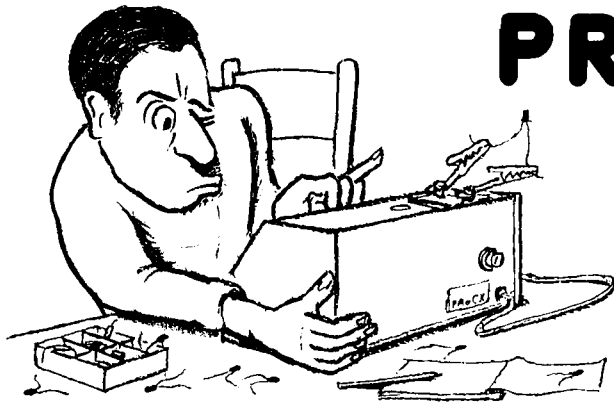


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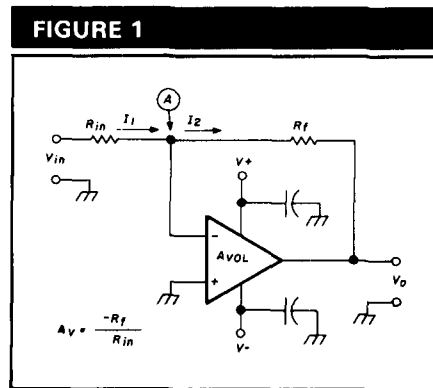
Overview of Operational Amplifiers: Part 2 — Inverting and Noninverting Follower Circuits

Last month I gave you the basics of the operational amplifier and other linear IC devices. I discussed the properties of the ideal op amp, and some common problems that represent departures from that ideal. This month I'll take a look at the standard circuit configurations and the derivation of transfer functions. Let's start with the inverting follower configuration.

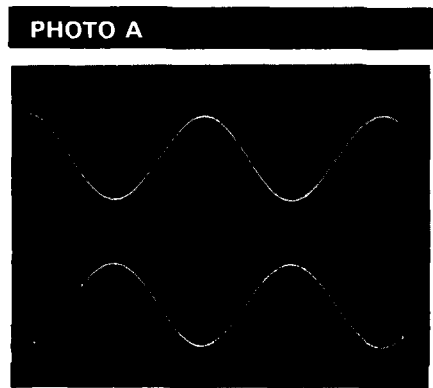
Inverting follower circuits

Figure 1A shows the inverting follower circuit. It is characteristic of an inverting follower that the output signal is 180 degrees out of phase with the input signal (photo A). The transfer function is $A_v = V_o/V_{in}$.

The noninverting input is grounded in the inverting follow circuit, so you must treat the inverting input as if it were also grounded. Ideal property number 6 (see last month) requires that the inverting input be treated as if it were also grounded, as at zero volts potential. This gives rise to a somewhat confusing concept — virtual ground. The inverting input isn't actually grounded, but since it's at zero potential because the other input is grounded, you can say that it is "virtually" grounded. The concept is simple; only the semantics are confusing.



Inverting follower circuit.



Input (top) and output (bottom) waveforms of a gain of -1 inverting follower.

Let's consider the currents appearing in node "A" of fig. 1. You know from ideal property number 3 (Z_{in} is infinite) that I_3 , the input bias current, is zero. You also know from Kirchoff's Current Law (KCL) that all currents into and out of a junction algebraically sum to zero. Thus,

$$I_1 = -I_2 \quad (1)$$

You also know from Ohm's law that

$$I_1 = V_{in}/R_{in} \quad (2)$$

and,

$$I_2 = V_o/R_{in} \quad (3)$$

Thus, when you substitute these two equations into KCL:

$$(V_{in}/R_{in}) = -(V_o/R_f) \quad (4)$$

You know that a voltage amplifier's transfer function is:

$$A_v = V_o/V_{in} \quad (5)$$

Solving eqn. 4 for the transfer function (eqn. 5) yields:

$$V_o/V_{in} = -R_f/R_{in} \quad (6)$$

Thus, the voltage gain A_v of the inverting follower is given by the ratio of two resistors:

$$A_v = -R_f/R_{in} \quad (7)$$

You can design the inverting amplifier by manipulating the values of these two resistors (see fig. 1). That's the exciting part of op amp theory, and what makes the device so simple to apply.

There's a constraint on the minimum allowable value of R_{in} . Point A is virtually grounded, so the input impedance of this circuit is the resistance of R_{in} . One rule of thumb of voltage amplifier design says the input impedance of a stage must be five times (some people, myself included, prefer ten times) the source impedance of the signal source.

Example:

Design a gain of 100 inverting amplifier that has an input impedance of 10k or more.

Solution:

Since the input impedance must be 10k, R_{in} must be 10k or more. Set it

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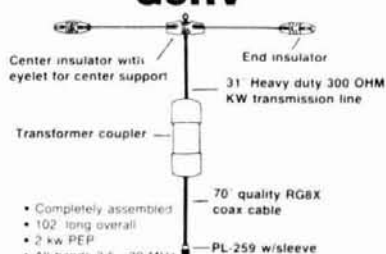
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at 10k. Solving the gain equation for R_f yields:

$$R_f = A_v \times R_{in}$$

$$R_f = (100) \times (10,000 \text{ ohms})$$

$$R_f = 1,000,000 \text{ ohms}$$

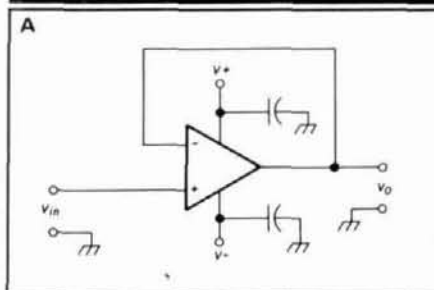
So, a 10k input resistor and a 1 meg feedback resistor yield a gain of 100. Since this is an inverting follower, the gain is actually -100. (The "-" sign indicates the 180-degree phase reversal between input and output normal to inverting amplifiers.)

PHOTO B



Input (top) and output (bottom) waveforms of gain of +2 noninverting follower.

FIGURE 2



Unity gain noninverting follower.

Noninverting followers

The noninverting follower applies a signal to the noninverting input. The output signal is in phase with the input signal (zero degree) phase shift (photo B). There are two basic configurations for the noninverting follower:

- Unity gain noninverting follower
- Noninverting follower with gain.

Figure 2A shows the unity gain noninverting follower. The output terminal is connected to the inverting input, producing 100 percent feedback. The output voltage is equal to the input voltage. So of what use is a

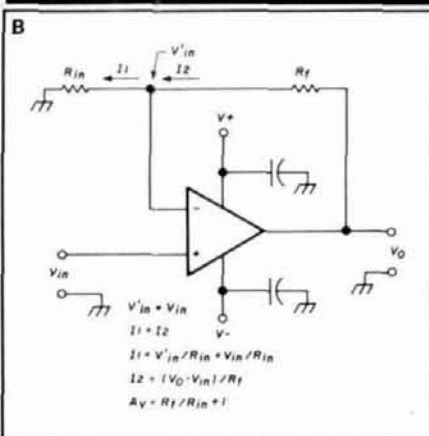
unity gain (i.e., gain of 1) voltage amplifier? There are three principal uses: buffering, impedance transformation, and power amplification. Buffering means using an amplifier to isolate a circuit from its load. Some oscillators and astable multivibrators change frequency if the load impedance changes, so a unity gain noninverting follower helps "buffer" the circuit. Also, some transducers with high source resistances load badly if not buffered by an extremely high input impedance amplifier; the crystal microphone is one example.

Impedance transformation occurs because the input impedance is very high, while the output impedance is very low. You can use this circuit when acquiring a signal from biological electrodes or chemical transducers, etc., where the source impedance is extremely high. A pH electrode, for example, has source impedances ranging from 10 to 100 megs.

The voltage amplification is unity. This is illustrated by the fact that the voltage remains constant ($V_o = V_{in}$). Consider also that the impedances are unequal. Obviously, since power is defined by $P = V^2/R$, reducing R while keeping V constant results in higher power (P).

The noninverting follower with gain circuit in fig. 2B retains the properties of the unity gain circuit, but produces voltage gain as well. Keep in mind that the inverting input (point A) is at V_{in} . Analysis similar to the previously used

FIGURE 2



Noninverting follower with gain.

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method produces a voltage gain of:
 $A_v = (R_f/R_{in}) + 1$ (8)

The noninverting follower circuits are used wherever extremely high input impedance is needed, or where no phase reversal can be tolerated. In communications circuits the noninverting gain follower is often used for audio microphone preamplifiers.

Operation from a single power supply

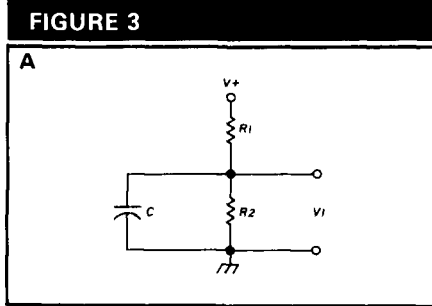
Operational amplifiers are normally operated from a bipolar DC power supply. Such a power supply has $V+$ and $V-$ voltages that are each referenced to common. This system essentially requires two independent DC supplies. In some cases, however, either ultimate use or other design constraints lead to the necessity of a single (monopolar) DC power supply. An example is +13.8 mobile circuits. In this section I'll discuss simple methods for operating the amplifier from a single DC power supply.

Some schemes exist for creating a split power supply from a monopolar one in order to mimic bipolar power supply operation. One scheme connects two zener diodes in series across the single supply, along with the necessary current-limiting resistors. The junction between the two zener diodes becomes the signal common. A severe limitation of this method is that the DC supply common can't be chassis referenced.

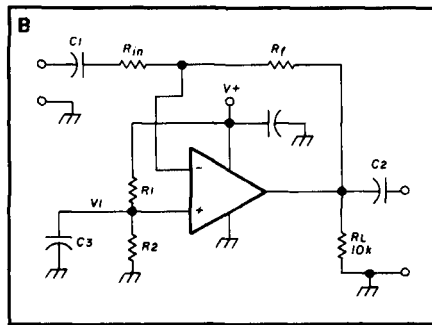
Another scheme is to use the regular monopolar DC power supply for $V+$, and a DC-to-DC converter circuit for $V-$. Such a circuit is little more than an AC or square wave oscillator in the 20 to 500-kHz range, with its output signal rectified and filtered to produce the $V-$ voltage.

Figure 3A shows the method for biasing the operational amplifier inputs to permit single supply operation. This technique is based on the simple resistor voltage divider circuit in fig. 3A. The output voltage (V_1) is given by the standard voltage divider equation:

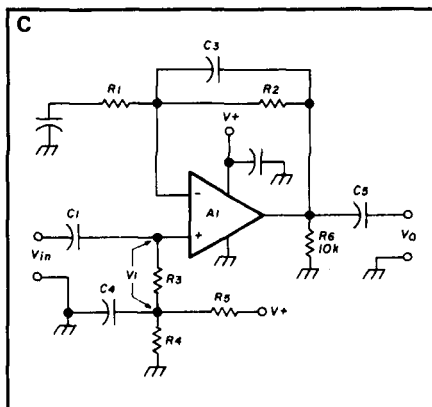
$$V_1 = \frac{R_2 \times (V+)}{R_1 + R_2} \quad (9)$$



Resistor voltage divider.



Inverting follower operated from single supply.



Noninverting follower operated from single supply.

In most cases, the value of V_1 will be one-half $V+$, so the operational amplifier has a quiescent output point that is midway between extremes. This bias level is achieved by making $R_1 = R_2$. The value of R_1 and R_2 is usually selected so that it falls between 1k and 100k. The capacitor shunting resistor R_2 is used to decouple AC variations on the power supply line. The capacitance value is selected for a reactance value of one-tenth R_2 (i.e., $R_2/10$) at the lowest frequency of operation. For example, suppose $R_2 = 10k$, and the lowest frequency of operation is 10 Hz. If R_2 is 10k, then the capacitive reactance of the shunt capacitor should be:

$R_2/10 = (10k)/10 = 1k$. Solving the usual capacitive reactance equation for C gives you:

$$C_{\mu F} = \frac{1,000,000}{2 \pi F X_c} \quad (10)$$

$$C_{\mu F} = \frac{1,000,000}{(2)(3.14)(10 \text{ Hz})(1000 \text{ ohms})}$$

$$C_{\mu F} = \frac{1,000,000}{62,800}$$

$$C_{\mu F} = 15.9 \mu F$$

The value $15.9 \mu F$ is non-standard, so you'd select a 16, 20, or $22 \mu F$ standard unit.

Figure 3B shows the method for biasing an operational amplifier in the inverting follower configuration. In the bipolar supply version of this circuit the noninverting input is grounded (i.e., set to zero volts). But in single supply operation, you apply bias voltage V_1 to the noninverting input. This voltage (V_1) also appears on the inverting input, making DC blocking capacitor C_1 necessary. The output terminal is biased according to the value of V_1 , and may also require a DC blocking capacitor (shown in fig. 3C) if such a voltage adversely affects the following stage.

Select the value of capacitor C_1 to have a low impedance at the lowest frequency of operation, using a protocol similar to that discussed for the voltage divider shunt capacitor. A general rule of thumb is to regard $R_{in}C_1$ as a high-pass filter with a cut-off frequency, F_c , equal to $1/(6.28 R_{in}C_1)$. The object is to choose a value of C_1 , given a value for R_{in} , that results in a value of F_c lower than the lowest operating frequency.

The circuit configuration for noninverting follower circuits is shown in fig. 3C. This circuit is the same as for inverting followers, except for resistor R_3 . The purpose of R_3 is to maintain a high input impedance to signals applied to the noninverting input. The minimum value of R_3 is at least ten times the output resistance of the driving stage. In practical cases, however, the source impedance is usually low enough that it's possible to set R_3 to

100 or 1000 times the source impedance. Typical values range from 10k to 1 meg, with 100k predominating.

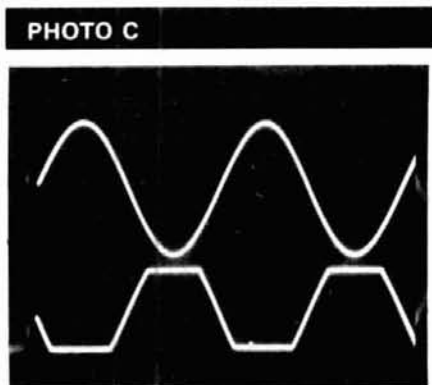
Select the value of C1 so that the cutoff frequency of the filter formed by C1R3 is lower than the lowest operating frequency. The same equation applies here as before. Use capacitor C4 and resistor R4 when the $(V+)/2$ bias on the output terminal will adversely affect a following stage or instrument. Again, the "lowest frequency of operation" rule is invoked when setting the value of C1, with the resistance being the input resistance of the following stage.

Some common problems

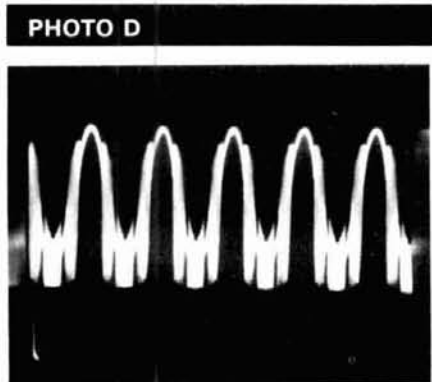
I find it almost impossible to wire up a circuit without making at least one mistake. Check your wiring before applying power to the circuit. Fortunately, most op amps will survive a whole host of errors — *except* reversed DC power supply polarity!

Before applying power you'll need to check a few things. Don't send a signal until after power is applied. Ground the input to simulate a signal of zero volts. Next, turn on the power and use a DC voltmeter to check the $V-$ and $V+$ power supplies. Make sure these potentials are proper. Now check the output terminal. It should be 0 Vdc if you use bipolar supplies, or at the potential set by the voltage divider if you do otherwise ($1/2 - (V+)$ is common). If all's well, turn on the signal and check the circuit operation. If not, then turn off the power and look for the problem — you've probably miswired something. (An op amp from a "cheapie" source may well be defective.)

Photo C shows the result when the amplifier inputs are overdriven for the circuit conditions. Three factors can lead to the clipping shown in the output signal (lower trace). The first is excessive input signal. (This situation can also be dangerous to the op amp's health.) The second is a value that's too low for the DC power supplies (e.g., ± 6 Vdc when ± 10 volt output signals might be expected). The third factor is a gain that's too high for the



Input (top) and output (bottom) waveforms of an overdriven amplifier showing "clipping."



Ooops! Forgot the decoupling capacitors! power supply value (i.e., when the $V-$ and $V+$ supplies are maximum).

Photo D shows oscillation superimposed on a sine wave output signal. I took this photo from an oscilloscope connected to the output of a 741 amplifier in which the decoupling capacitors on the $V-$ and $V+$ power supplies were missing. The solution is to place at least some decoupling at each op amp terminal as close as possible to the body of the device. Note that 741 devices are called "unconditionally stable" in some texts, so some people believe that they won't oscillate.

Conclusion

Applying operational amplifiers is easy. The one simple rule to remember is that the output/input transfer function is governed by the feedback network. For simple voltage amplifiers you need only remember that the ratio of the resistors is the determining factor. For AC amplifiers you'll also need

to crank in the bypass capacitor values.

This article is based on my new book: *IC User's Casebook* (Sams No. 22488), available from the *HAM RADIO* Bookstore for \$12.95, plus \$3.50 shipping and handling. I can be reached at POB 1099, Falls Church, Virginia 22041, and would like to have your comments and suggestions for this column.

Article 1

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THE WEEKENDER



Get the most from your NiCds.

One way to maximize the useful life of your NiCds is to use them; they thrive on it! Part of this use should include full discharge and full charge cycles.

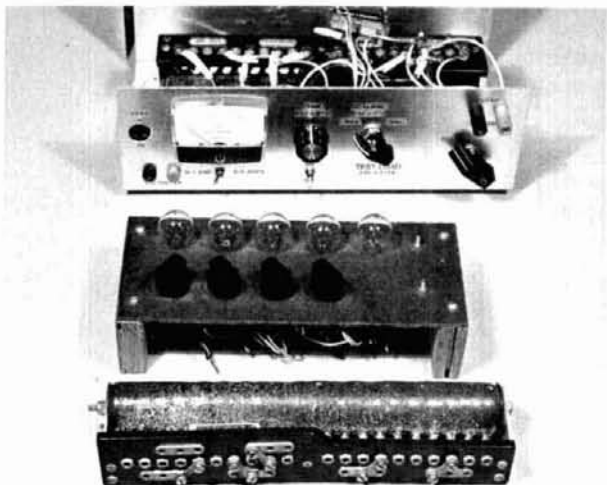
Many devices using NiCds come with a charger. Proper charging is usually easy to accomplish; it's simply a matter of charging them for a fixed period of time — often 16-20 hours. Proper discharge is not quite as easy to achieve.

My first experience with NiCds was in 1960. The military used NiCd wet cells to power selected equipment. These NiCd power supplies were stored fully discharged and shorted. They were removed from storage periodically, checked for proper electrolyte level, and charged. Then they were discharged at a specific load for a specific time to test their capacity. Individual cell voltages were checked during the discharge cycle, and any cells which discharged prematurely were removed and replaced. The battery was again charged and given the timed discharge test to be sure that it met the capacity requirements. A NiCd battery is only as good as its weakest cell. I have some of those early NiCd cells. They're now about 30 years old, but still usable!

The first commercially available NiCds I purchased in the mid-sixties were C and D cells. I periodically ran discharge capacity tests, almost from the time I bought them. I dated and numbered each cell so that I could track its performance. Some of those cells lasted over 10 years. I've found that neither age nor number of

By **W. C. Cloninger, Jr., K3OF**, 4409 Buckthorn Court, Rockville, Maryland 20853

PHOTO A



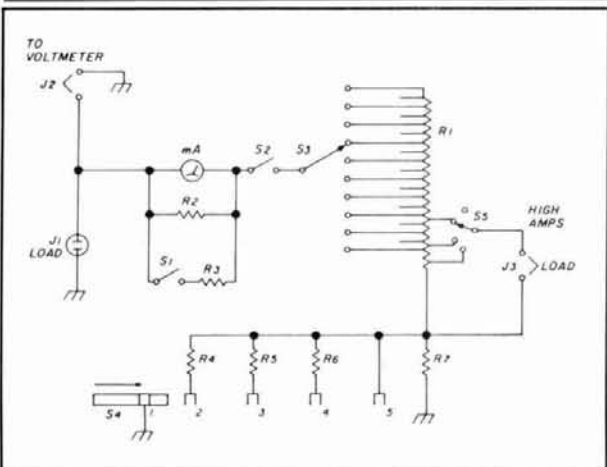
Multi-purpose test load is just a special purpose resistance substitution box.

PHOTO B



The multi-tapped resistor is the heart of the test load. Note the heavy-duty switch at the upper right for high amps.

FIGURE 1



Simple circuit for old-fashioned resistance-substitution box.

cycles is necessarily an indicator of when a NiCd cell needs to be replaced.

For years I discharged NiCds with almost anything

that would place a suitable load on them. I used flash-light bulbs, automotive accessories, high-wattage resistors, and 12-volt automotive bulbs. I also used an assortment of clip leads, ammeters, voltmeters, and battery holders. It was a mess, but it worked! There are still times when I use a gang of automotive bulbs (photo A).

I had known for years that it would be nice to have a clean, functional test load. I spotted a multi-tapped 200-watt 6.5-ohm resistor in a catalog.¹ A year or so later I ordered two of the resistors. I looked at them for another year. Then, one weekend I finally constructed my test load (photo B).

The circuit shown in fig. 1 is simple; it's basically an old-fashioned resistance substitution box. But remember, all power from the discharge of the NiCd battery is dissipated in heat, so the resistors must be capable of handling the required power level. The power dissipation is calculated with either $P=IE$ or $P=I^2R$. A 13.8-ohm load across 13.8 volts

$$(I = \frac{E}{R}, I = \frac{13.8}{13.8} = 1 A)$$

equals 13.8 watts ($P=1 \times 13.8 = 13.8$ watts). Because five resistors (R1, R4, R5, R6, and R7) share varied amounts of the 13.8 watts, no resistor needs to be rated over 10 watts. Switch S4 is a shorting type; I used it because that's what I had in my junkbox. If you use a non-shorting switch, calculate the values and maximum load on any single resistor and use a

TABLE 1

Approximate resistance ranges of switch S4 when used with switch S3 for fine adjustment.

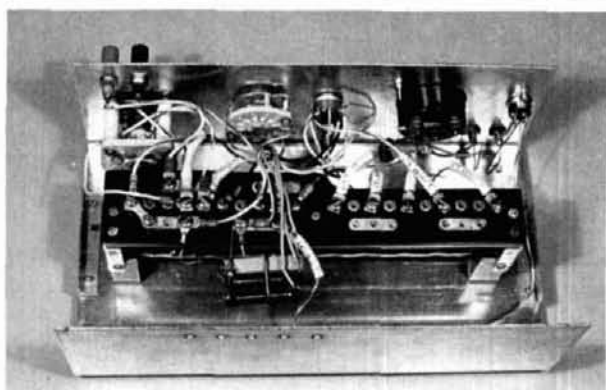
Range 1	1.1– 7.0 ohms
2	9.8–15.6 ohms
3	16.6–22.4 ohms
4	24.1–29.8 ohms
5	31.2–37.0 ohms

higher wattage resistor where required. Table 1 gives the approximate resistance ranges of switch S4, when used with switch S3 for fine adjustment.

Construction

There's nothing special about the construction (photo C). Just about everything I used came from my junkbox. R1 is the only component purchased specifically for this project. Even the wires with the terminals were "cut-offs" from disassembled equipment. Switches S3 and S4 were what I had available. The meter is a 0-1 mA movement with shunts for 0-1 and

PHOTO C



Foreground: Load resistor R1 before installation. Center: 10-A continuous-duty test load is guaranteed to brighten up your shack.

PARTS LIST

R1	6.5 ohm 200 watt multi-tapped resistor*
R4	100 ohm 10 watt
R5	50 ohm 10 watt
R6	20 ohm 10 watt
R7	30 ohm 10 watt
S3	10 pole rotary switch
S4	5 pole shorting rotary switch
S5	4 pole high amp ceramic switch
Meter	0-1 mA, or to suit
R2,R3	shunt resistors to suit meter
J1,J2,J3	Jacks to suit needs

*H & R Corporation, 401 E. Erie Avenue, Philadelphia, Pennsylvania 19134

Part number TM23K513. \$5.50 in December 1986 catalog.

0-2 A. The shunts are lengths of resistance wire removed from some old wire-wound resistors.

Start by connecting one end of the resistor wire to the meter. Use a clip lead on the other terminal of the meter, and slide the other end of the clip lead along the resistance wire until you get the proper reading. (Place another ammeter in series for reference.) Solder a wire to the resistance wire at this point, and connect the wire to the meter. I added switch S1 and another shunt resistor to give the meter two ranges. The tip jacks for an external voltmeter were added as a convenience as was switch S2, which allows the load to be turned off or on without disturbing the load settings.

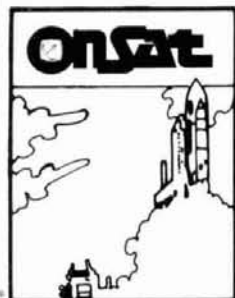
I also needed a high amp load capability to make power supply tests, so I added a second load circuit consisting of switch S5 and jack J3. The high amp section will handle loads of about 5 to 15 amps on a 13.8-volt power supply. Fifteen amps at 13.8 volts is pushing the rating of R1 and is used only for short times.

Using the test load

The capacity of NiCd cells is usually stated for the 1-hour discharge rate. That is, a 450-mAh (milliamp hour) AA cell will support a 450-mA load for one hour if it's fully charged and has 100 percent capacity. C

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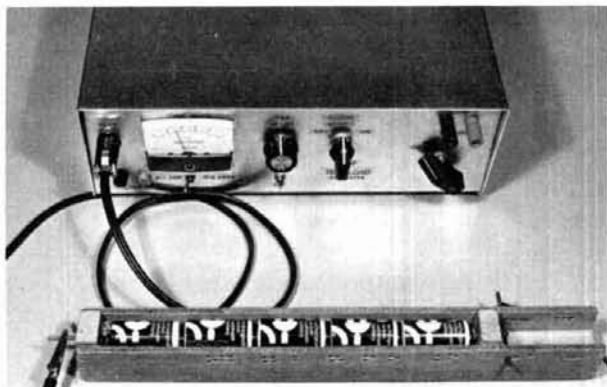
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PHOTO D



Discharge capacity test using adjustable battery holder.

and D cells are typically 1200 mAh (1.2 Ah). For capacity tests, I use the 1C rate (one times capacity); i.e., 450 mA for AA cells.

The first step is to discharge all cells. I use a homemade battery holder (**photo D**) for single cells. It's easy to check each cell voltage individually with a voltmeter during discharge. One of the advantages of a NiCd cell is a relatively flat discharge curve. Notice, I said "relatively" flat. Voltage under 1C load will be about 1.2 volts for a long time. As it nears discharge, it will drop to 1.1 volts and — a very short time later — to 1.0 volt. The change in voltage at near discharge can take place in a matter of a few minutes, so watch the cells carefully. This isn't a "set it and leave it" test procedure. At 1.0 volt you can consider the cell discharged and pull it. However, don't let the cell drop below 1.0 volt, or it might reverse polarity and not recover when recharged. If you're discharging a fixed battery, like an HT battery pack with seven cells (8.4 volts nominal), stop the discharge when the battery reaches 7.0 volts, or 1.0 volt per cell average.

Fully charge the cells or battery as recommended and you're ready for the discharge capacity test. I connect a digital voltmeter to the jacks on the test load to monitor total voltage. If I'm testing an HT battery pack, this is the only voltmeter I'll need. If I'm testing a group of individual cells as shown in **photo D**, I use a second voltmeter to monitor and pull individual cells whenever they drop to 1.0 volt.

Turn on the test load and set for 1.2 A (for 1.2 Ah cells). Be sure to log in the start time, or use a stopwatch or timer. You'll have to readjust the test load as voltage drops to maintain a constant load. If the first cell takes 45 minutes or 0.75 hours to drop to 1.0 volt, multiply the 1.2 A load times 0.75 hours. The capacity of that cell is 0.9 Ah or 75 percent of rated capacity. I pull each cell as it reaches 1.0 volt and calculate its capacity. Use the same time/load procedure to discharge a battery pack, but stop when the volt-

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age drops to 1.0 volt times the number of cells in the battery pack. The same quick calculation will give you the capacity of your battery pack.

I keep records on my cells and battery packs. The original, and only, battery pack for my TR2500 HT is almost 4 years old but still has over 80 percent of its original capacity. As cells get older, they may not hold 1.2 volts at load for as long, but may drop slowly to and through the 1.1-volt range. In other words, the cell can no longer hold the relatively flat discharge curve. Such cells may or may not be suitable, depending on the type of equipment in which they are used. In any case they are "suspect," and should be watched more closely than normal.

You may also want to let fully charged NiCd's sit for up to 30 days, run a discharge test, calculate the capacity, and compare it to the capacity of the cells or battery when just charged. The results of age or premature self-discharge can be quite noticeable here.

Remember, your NiCd's actually *like* this kind of testing. In fact, a couple of complete charge/discharge cycles may actually improve their capacity. And...you'll have the added benefit of knowing just what condition they're in!

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cumulative index

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ANTENNAS AND TRANSMISSION LINES

general

Antenna insulators, PTFE VHF
W5JTL p 98, Oct 85

Antenna relay sequencing
KN5SS p 17, Oct 87

Antenna support (HN)
W6XM p 64, Jun 84

Applied Yagi antenna design part 2: 220 MHz and the Greenblum design data
WB3BGU p 33, Jun 84

Balun chop suey
K4KJ p 113, May 85

Bulkhead connector (HN)
K9CZB p 78, Apr 85
Short Circuit p 74, Jul 85

Compact travel antenna
K1BQT p 29, Jun 87

Construction techniques using PVC pipe to make antennas
W2OQI p 98, Sep 88

Direction-finding tool, the fox box
K1ZJH p 25, Oct 85

Easy measurement of antenna currents (HN)
KO1F p 39, Sep 88

Elmer's notebook: Standing wave ratio—what does it mean?
W1SL p 98, Feb 88

Groundplane antenna
Comments: DJØTR/OE8AK p 6, June 87
Comments, ground plane antennas
W6BCX p 6, Oct 87

Ground rod resistance
K4MT p 95, Jul 84
Comments p 8, Sep 84

Ham Radio techniques
W6SAI p 75, Nov 84

Ham Radio techniques
W6SAI p 67, Dec 84

Ham Radio techniques: antenna systems
W6SAI p 55, May 87

Ham Radio techniques: A look at the groundplane antenna
W6SAI p 38, Oct 88

Homebrew antenna mount
W6QIR p 35, May 87

Leyden's magic jar: the derivation of the Hertzian and Marconi antennas
KR6A p 24, Oct 84

Preampifiers, Active antenna
RW Burhans p 47, May 86

Practically speaking: using antenna noise bridge
K4IPV p 69, May 86

Secrets of successful low-band operation: part 1
K2RR p 16, May 86

Secrets of successful low-band operation: part 2
K2RR p 17, Jun 86

7/8-inch hardline coax connectors—construct at your own low cost
WA5FAC p 95, Sep 88

VHF/UHF world
W1JR p 110, May 84

VHF/UHF world
W1JR p 77, Sep 86

Wire plow, build a simple
W7IV p 107, May 84

Yagi design program
W6NBI p 6, May 87

Yagis, stacking is a science
K1FO p 18, May 85

Yagi vs Quad, part 1
K2SS p 68, May 88

Yagi vs Quad—part 2
K2SS p 78, Jun 88

hf antennas

Active antenna, 0.5-30 MHz
K1ZJH p 37, May 85
Comments, Hansen, R.C. p 10, Jul 85

Analyzing 80-meter delta loop arrays
K1GQ p 10, Sep 86

Applied Yagi antenna design, part 6: the model and a special teaching tool
WB3BGU p 89, Oct 84

Capacitively loaded dipole, high-performance
W6VX p 33, May 84

Delta loop, the reduced-size, full-performance, corner-fed
G3TKN p 67, Jan 85

Designing trap antennas: a new approach
WØJF p 60, Aug 87

Designing Yagis with the Commodore 64
NØCAO p 107, Jan 86

Elmer's notebook: ten-meter skyware
W1SL p 90, Jul 88

End-fed 8JK; switchable vertical array
W1JF p 53, May 85

Five-band dipole
W6HPH p 76, Sep 88

Ham Radio techniques
W6SAI p 65, Jan 84
Comments, WA2DRL p 8, Sep 84

Ham Radio techniques
W6SAI p 63, Feb 84
Comments, K4KYV p 12, May 84
Comments, WD6DUD p 8, Sep 84
Comments, AD1G p 5, Dec 84

Ham Radio techniques
W6SAI p 53, Mar 84

Ham Radio techniques
W6SAI p 76, Apr 84

Ham Radio techniques, fifty years ago
W6SAI p 58, Jun 84

Ham Radio techniques, 160 redux
W6SAI p 89, Jul 84

Ham Radio techniques
W6SAI p 96, Aug 84

Ham Radio techniques
W6SAI p 106, Oct 84

Ham Radio techniques
W6SAI p 55, Dec 85

Ham Radio techniques: time and frequency station WWVS, minibeam design, "white noise"
W6SAI p 37 Jun 87

Ham Radio techniques: 80-meter antenna, 160-meter discone antenna
W6SAI p 57 Jul 87

Ham Radio techniques: antennas
W6SAI p 57 Sep 87

Ham Radio techniques: "radio ground" on 160 meters
W6SAI p 53, Mar 88

Ham Radio techniques: why not a two-element Yagi
W6SAI p 36, May 88

Ham Radio techniques: a nifty bi-square beam for 10 or 12 meters
W6SAI p 68, Jun 88

How high should your HF antenna be
W5QJR p 89, May 86

Inverted "L", limited space (HN)
W8FR p 63, Jun 84

JR vari-lobe antenna, control your take-off angle
W1JF p 46, May 85

Matching dipoles (letter)
W5XW p 8, Aug 85

Modified Bobtail (HN)
WØMBP p 87, Sep 84

Multiband 8JK, an end-fed
G3SBA p 81, May 84

New class of directive antennas
W4MB p 107, Apr 86
Comment, AG4R p 9, Jul 86

No-compromise, multiband, low VSWR dipole
GM3HAT p 69 May 87

Odd antennas, comments
W9RXC p 9, Aug 86

Offset drooper: an improved ground plane
W6BCX p 43, Feb 86

Old antennas, comments
WØMBP p 9, Feb 86

Optimizing gain on Yagi antennas
K2SS p 21, Mar 88

Phased arrays, feeding:
K8BI p 58, May 85
Short circuit p 74, Jul 85

Quad antenna: part 1—general concepts
W4MB p 43, May 88

Quad antenna: part 2—circular and octagonal loops
W4MB p 54, June 88

Quad antenna: part 3—circular loop and octagonal arrays
W4MB p 34, Aug 88

Rhombics, controlled vertical radiation, part 1: designing for high performance
N4JH p 100, Mar 85

Rhombics, controlled vertical radiation, part 2: antenna erection and performance
N4JH p 99, Apr 85

Secrets of successful low-band operation: part 1
K2RR p 16, May 86

Secrets of successful low-band operation: part 2
K2RR p 17, Jun 86

SEED antenna: a short, efficient end-fed dipole
W4JAZ p 103, Sep 84

Shortened 40-meter four-element sloping dipole array
OE5CWL p 74, May 88

Structural evaluation of Yagi elements
K5IU p 29, Dec 88

Tapered vertical, calculating the input impedance of
K3OQF p 24, Aug 85
Short circuit p 78, Oct 85

Terminated vee beam, sloping
Ross, Robert p 71, May 85

Three-band sloper for 7, 18 and 24 MHz (HN)
W5FG p 58, May 88

Top-loaded vertical, a high-efficiency
W6US p 65, Oct 84

Transmission line antenna, 160-meter
N9NB p 87, May 85

Trap antenna, design your own
W4MB p 37, Oct 84

Two-element hf beams
G6XN p 8 May 87
Comments, W9OAM p 10, Mar 84

Two single 80-meter radiators for short and long skip (HN)
YO4WU p 98, Nov 88

Vertical phased arrays: part 6
K2BT p 45, May 84

Verticals over REAL ground
W89VWA p 35, Jan 84

W2PV 80-meter quad
K1GQ p 56, May 86

W8JK antenna for 40, 30 and 20 meters
N6YC p 9, May 88

Yagis, stacking is a science
K1FO p 18, May 85

3-element Yagi design, key to
K3OQF p 48, Mar 84

40, 80, and 160-meter vertical, remote controlled
W7LR p 38, May 84

80-meter half-wave sloper uses reflector (HN)
KO1F p 48, Oct 84
Short circuit p 8, Feb 85

vhf antennas

Antenna insulators, PTFE VHF
W5JTL p 98, Oct 85

Applied Yagi antenna design part 1: a 2-meter classic revisited
WB3BGU p 14, May 84

Applied Yagi antenna design part 2: 220 MHz and the Greenblum design data
WB3BGU p 33, Jun 84

Applied Yagi antenna design part 3: 432 MHz with Knadle and Tilton
WB3BGU p 73, Jul 84

Applied Yagi antenna design part 4: a 50-MHz Tilton/Greenblum design
WB3BGU p 103, Aug 84

Applied Yagi antenna design part 5: additional optimization techniques
WB3BGU p 93, Sep 84

Colagi antenna, The
VE3BFM p 61, May 86

Computer-aided design of long VHF Yagi antennas
VK4ZF p 28, May 86

Cylindrical feedhorns revisited
WA9HUV p 29, Feb 86

Efficiently launch-VHF/UHF wave
W3HWC p 63, Oct 88

Fastening Trigon reflectors to VHF antennas (HN)
W5JTL p 88, Sep 84

Ham notebook: a 2-meter halo antenna
NR5A p 63, May 87

High-performance Yagis for 432 MHz
K1FO p 8, July 87
Short Circuit p 97, Oct 87
Comments: KLM balun
WMSScott p 6, Sept 87

Long 2-meter collinears—a simple way to achieve gain (HN)
WB3AYW p 5, May 86

VHF/UHF World
W1JR p 110, May 84

VHF/UHF World: stacking antennas, part 1
W1JR p 129, Apr 85

VHF/UHF World: stacking antennas, part 2
W1JR p 95, May 85

VHF/UHF world
W1JR p 85, Dec 85

VHF/UHF world: Designing and building loop Yagis
W1JR p 56, Sep 86
Short circuit p 54, Jan 86

VHF Yagi CAD on the C-64
W4PFZ p 70, Sep 86

VHF/UHF world: Yagi facts and fallacies
W1JR p 103, May 86

VHF/UHF world: optimized 2- and 6-meter Yagis
W1JR p 92, May 87
Short circuit p 41, Aug 87
Short circuit p 49, July 87

Aries-1 Amateur Radio Integrated Entry System

ALL MODE

ID(Sta): WOABC Name: CHAR City: DENVER State: CO
 Date: 08-10-88 Begin: 21:05 End QSO: 21:07:22 Freq: 28.485.0
 Type (mode): USB My RST: His RST: 59 Power: QSL:
 Remarks:
 Data: **Data Base / Status Window**
 Status: [T/R] [CLS] Manual Mode [CLD] [Sp/F] [Qu/eX]

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✓ 167

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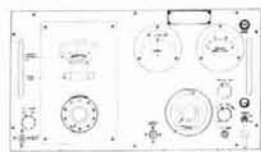
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✓ 168

VHF/UHF world: minimum requirements for 2-meter EME-part 1
 W1JR p 39, Aug 87
 Yagi triangular array
 W2KJP p 42, May 87
 Yagi trigon reflector, Optimizing
 WB3BGU p 84, Jan 86
 Yagi, a high-gain 70-cm
 W1JR p 75, Dec 86
 Short circuit:
 p 68, Feb 87
 Yagis, stacking is a science
 K1FO p 18, May 85
 2-meter J-pole antenna, all-metal
 KD8JB p 42, Jul 84
 Comments, K2WWT,
 KD8JB p 8, Feb 85
 Comments, DJ0TR/OE8AK p 8, Nov 85
 2-meter V-antenna
 AD1B p 86, Jan 84

matching and tuning

Antenna matching, easy
 WB4GCS p 67, May 84
 Broadband RF transformers
 K2LB p 75, Jan 86
 Designing trap antennas: a new approach
 W0JF p 60, Aug 87
 Elmer's notebook: antenna tuner
 W1SL p 83, Apr 88
 Elmer's notebook: antenna tuner
 W1SL p 102, May 88
 Gamma matching, basic
 WB0KN p 29, Jan 85
 Gamma matching programs for the C-64/128
 N0CAO p 87, May 87
 Ham radio techniques
 W6SAI p 65, Jan 84
 Comments, WA2DRL p 8, Sep 84
 Ham radio techniques
 W6SAI p 63, Feb 84
 Comments, K4KYV p 12, May 84
 Comments, WD6DUD p 8, Sep 84
 Comments, AD1G p 8, Dec 84
 Ham Radio techniques: "radio ground" on 160 meters
 W6SAI p 53, Mar 88
 Improving operation with the MFJ 989
 Transmatch (Weekender)
 W4RNL p 24, Nov 88
 Matching dipole antennas
 W1DLP p 129, May 84
 Comments, W5XW p 12, Apr 85
 Phased arrays, feeding: an alternative method
 KB8I p 58, May 85
 Short circuit p 74, Jul 85
 Pi network equations
 K4MT p 109, Oct 88
 Practically speaking: impedance matching
 K4IPV p 27, Aug 88
 Remote tuner for 75-meter mobiles (weekender)
 K9MLD p 36, Oct 88

towers and rotators

Antenna tower, fixed, tilt-over conversion
 PA0SE p 125, May 85
 AUTOTRAK, a simple rotor interface board for the C-64, VIC-20 and applicable to other popular computers
 K7NH p 10, Dec 87
 Ham notebook: simple tower guards
 K1ZJH p 39, Sept 88
 Match your antenna to your tower
 WD0QGF p 14, Jun 84
 Tower installation: make it sturdy, make it safe
 WB5IR p 22, Jun 84
 Turning that big array
 VE3AIA p 10, Jun 86
 Keep your tower up
 KB9IW p 26, Jun 84
 UHF antenna tower, low-cost
 KA6GVY p 30, Oct 84

transmission lines

Artificial Transmission lines
 KA8OBL p 21, Jul 86
 Bridge measurements, the half-wave transmission line in (HN)
 K4KI p 108, Nov 84

Elmer's notebook: transmission lines
 W1SL p 90, Mar 88
 General purpose line transformers
 W6IOJ p 94, Aug 86
 Ham radio techniques, fifty years ago
 W6SAI p 58, Jun 84
 Measuring transmission line parameters
 OE2APM/AA3K p 22, Sept 88
 Open-wire line for 2 meters
 N4UH p 94, Jan 87
 Practically speaking: transmission lines and their typical AC responses
 K4IPV p 34, Sept 88
 Practically speaking: standing waves-a review
 K4IPV p 85, Oct 88
 Real coax: impedance and phase relationships
 K2BT p 8, Apr 87
 Short circuit p 91, Jul 87
 Practically speaking: amplifier tuning problem
 K4IPV p 78, Nov 86
 Real coax: impedance and phase relationships
 K2BT p 8, Apr 87
 Short circuit p 91, Jul 87
 RF transmission cable, microwave applications
 K3HW p 106, May 85
 Solving transmission line problems on your Commodore 64
 K9CZB p 74, May 86
 Short circuit p 87, Jul 86
 VHF/UHF World-transmission lines
 W1JR p 83, Oct 85
 Comments W9ICZ p 9, Apr 86
 VHF/UHF World
 W1JR p 85, Dec 85

AUDIO

Advanced CW processor
 W6NRW p 25, Dec 86
 Audio Filter design, computer-aided
 KE2J p 15, Oct 85
 Audio filter design, elliptic lowpass
 W3NQN p 20, Feb 84
 Audio oscillator to pulse generator conversion (HN)
 W0DLQ p 50, Oct 84
 Audio to microwave amplifier, build your own
 Gruchalla, Michael p 12, Mar 84
 Aural vco provides relative metering
 K1ZJH p 97, Jan 87
 Automatic gain control, an audio
 K7NM p 24, Sep 84
 Build a QSO "beeper"
 KF6CU p 38, Jan 88
 Code practice oscillator (weekender)
 N2DCH p 65, Oct 88
 Converting mobile microphones for handheld VHF transceivers
 K08KZ, WB3JCC p 79, Mar 86
 Short circuit p 199, Aug 84
 Extended-range VU meter
 WB6JNN p 59, Sep 86
 Improving the audio on the ICOM IC-27
 K08KZ p 61, Feb 86
 Modifying microphones
 VE7CB/W6 p 81, Jan 87
 Passive audio filter design, part 2: highpass and bandpass filters
 Niewiadomski, S p 41, Oct 85
 Comments, W3NQN p 8, Nov 85
 Passive audio filter design: part 3
 Stefan Niewiadomski p 29, Jan 86
 Phone patches, building and using
 N6ARE p 34, Oct 85
 Power speaker enhances mobile operation
 K1ZJH p 83, Jan 88
 Processor for code tapes
 W4ULD p 61, Sept 88
 Repeaters, speech synthesis for
 N9EE p 79, Mar 84
 Sight and sound CW
 W6NRW p 10, Jan 88
 Telephone ring indicator, visual (HN)
 W2QLI p 62, Apr 84
 Understanding telephones
 N6ARE p 39, Sep 85
 Comments, KD7WL p 9, Apr 86

COMMERCIAL EQUIPMENT

Annunciator bell for the Kantronics
 KPC-2
 K1ZJH p 22, Aug 86
 Argonaut 509 conversion for 30 meters (HN)
 AA4LL p 49, Oct 84
 C-64 and GLB PK-1 interface circuit
 W2EHD p 87, Mar 87
 CAT control system for the Yaesu
 FT-757GX
 SM8CPI p 26, Nov 87
 Computer control of ICOM R-71, 271, 471, and 751 radios
 NG6Q p 47, Apr 86
 Extending receive coverage for the IC-02 and IC-04
 WB6GTM p 77, Jul 86
 Comments: WB6GTM p 6, May 87
 Ham radio techniques
 W6SAI p 63, May 84
 Ham radio techniques, fifty years ago
 W6SAI p 58, Jun 84
 Ham Radio Techniques: "white noise" revisited
 W6SAI p 79, Oct 87
 ICOM's newest transceiver
 N1ACH p 17, Mar 88
 Improved gain distribution for the Yaesu
 FT-726R
 K1ZJH p 53, July 87
 Comments: Kudos for Kantronics
 WB3EXR p 6, June 87
 Improving the audio on the ICOM IC-27
 K08KZ p 29, Jan 86
 KWM2, RIT for the (HN)
 KH6JF p 109, Jul 84
 Modifying the Trio-Kenwood TS-930S
 WB9BXT p 67, Apr 86
 Modifying the Yaesu FT-301 for 30-meter coverage
 AF9Q p 42, Mar 86
 More fixes for the IC22S VHF radio
 VE6ZS p 91, Oct 88
 More optional notes on the TS-930S
 W6FR p 23, Apr 88
 Practically speaking: now that the warranty has expired
 K4IPV p 67, Sep 85
 Comments, W5QJM p 8, Nov 85
 RDF, An improved
 K00V p 67, July 87
 Simple IC-735 to C-64 interface
 N7ICW p 39, Mar 87
 Simple modifications and adjustments for the TS-930S
 W6FR p 19, Apr 87
 Technology of commercial television part 2: hardware
 KL7AJ p 54, Jan 88
 Ten-Tec Corsair modification (HN)
 N3BEK p 62, Apr 84
 Thumbwheel frequency selector for the Yaesu FT-757GX
 KA9SNF p 33, Nov 87
 TR-2500/2600 2-channel programming (HN)
 K9MLD p 128, Oct 85???IF filter mod (HN)
 KB0CY p 125, May 84
 TS-930S headset audio, increased undistorted (HN)
 W6FR p 128, Oct 85
 Using an RTTY terminal unit with the Heathkit HD4040 TNC
 AA8V p 59, Aug 86

COMPUTER-AIDED DESIGN

Bandpass filter design, interdigital, computer-aided
 N6JH, Monemzadeh p 12, Jan 85
 Short circuit p 117, Jun 85
 Computer-aided design of long VHF
 Yagi antennas
 VK4ZF p 28, May 86
 Design a no-tune amplifier with your personal computer
 W7DHD p 8, Sep 87
 Designing Yagis with the Commodore 64
 N0CAO p 107, Jan 86
 Diagnostic serial data latch
 KA9SNF p 56, Apr 88
 Direct currents reduce core permeability
 K5BVM p 58, Jul 86
 Short circuit p 87, Jul 86

Elmer's notebook: modems and RS-232
 W1SL p 113, Oct 88
 Gamma matching programs for the C-64/128
 N0CAO p 87, May 87
 Ham notebook: rebuild your C-64 keyboard with C-? parts
 AF8B p 74, Feb 88
 Linear design by computer
 W4MB p 37, Feb 87
 Low-cost pc board layout software
 Freeman, Eva p 8, Oct 87
 Remote repeater programming using a computer and a telephone
 KD9BC p 89, Mar 86
 RF filters, Build narrowband
 WB4EHS p 10, Mar 86
 Short circuit p 36, Jun 86
 Solving transmission line problems on your Commodore 64
 K9CZB p 74, May 86
 Top-down filter design
 VE5FP p 41, Jan 87
 VHF Yagi CAD on the C-64
 W4PFZ p 74, May 86
 Comments: Yagi design program
 W6NBI p 6, May 87
 Yagis, designing with the Commodore 64
 WA3EKL p 59, Jun 85

CONSTRUCTION TECHNIQUES

Advanced CW processor
 W6NRW p 25, Dec 86
 Air-wound coils, constructing
 W7BKE p 37, Aug 84
 Battery charger, NiCd, constant current, a pulsed
 K2MWU p 67, Aug 85
 Build a better box
 Gruchalla, Michael p 45, Aug 84
 Build narrowband RF filters, Comments
 WB4EHS p 9, Sep 86
 Bulkhead connector (HN)
 K9CZB p 78, Apr 85
 Short circuit p 74, Jul 85
 Carpet samples in the ham shack
 K1ZJH p 82, Sep 87
 Code practice oscillator
 N2DCH p 65, Oct 88
 Construction techniques using PVC pipe to make antennas
 W2OOI p 98, Sept 88
 Cooling semiconductors part 1: designing and using heatsinks
 Martin, Vaughn D p 33, Jul 84
 Cooling semiconductors part 2: blowers and fans
 Martin, Vaughn D p 52, Aug 84
 Design an amplifier around the
 3CX1200A7
 W7DHD p 33, Dec 87
 DTMF tone signaling circuit
 WV6A p 42, Sept 88
 Dummy load, DC
 W4MLE p 91, Apr 85
 Elevation indicator, inexpensive
 W5JTL p 67, Jun 85
 Elmer's notebook: the mysterious "Q"
 W1SL p 110, Sept 88
 Get the most from your NiCds (Weekender)
 K3QF p 88, Dec 88
 G.O.E.S. reception: a simple approach
 WA4WDL p 46, Jan 84
 Ham notes: Waterproofing fittings
 W4MLE p 101, Nov 86
 High-frequency dummy load (HN)
 W1KWE p 64, Jun 84
 Homebrew tuning dial
 N2DCH p 75, Dec 88
 Homebrewing equipment from parts to metal work
 W7KBE p 26, Mar 88
 Inductance equation, a different approach (HN)
 K4KI p 116, Dec 84
 Junk-box ingenuity, how to buy, use, and recycle surplus electronic parts
 WB4EHS p 32, Aug 84
 Low-cost pc board layout software
 Freeman, Eva p 8, Oct 87
 Make a homebrew sheet metal brake for chassis construction projects
 WB6BH p 43, Jun 86
 Microstrip impedance program
 KBUR p 84, Dec 84
 NE5205 wideband amplifier
 Gruchalla p 30, Sep 86

Short circuit p 72, Jan 87
 New uses for old tuners
 W6WTU p 25 Jan 88
 Passive audio filter design, part 1: development and analysis
 Niewiadomski, S p 17, Sep 85
 Polymer film transforms mechanical energy to electrical energy
 WA4KFZ p 55, Dec 84
 Power FETs: trend for VHF amplifiers
 Peters, Daniel and W7PUA p 12, Jan 84
 Practically speaking: Keep it cool
 K4IPV p 75, Apr 86
 Practically speaking: parts sources
 K4IPV p 78, Nov 86
 Practically speaking: grounding and shielding, pt. 1
 K4IPV p 47, Apr 87
 Practically speaking: grounding and shielding, pt. 2
 K4IPV p 81, May 87
 Comments: grounding and shielding
 KA8DKT p 6, Aug 87
 Practically speaking: drift and shift
 K4IPV p 75, Jan 88
 Practically speaking: noise, signals and amplifiers
 K4IPV p 77, Feb 88
 Practically speaking: feedback
 K4IPV p 60, May 88
 Practically speaking: "ferriting" out the problem
 K4IPV p 72, Jun 88
 Practically speaking: non-ideal linear IC amplifiers typical problems and how to solve them
 K4IPV p 72, Jul 88
 Practically speaking: Overview of op amps-part 1
 K4IPV p 100, Nov 88
 Practically speaking: Overview of op amps-part 2
 K4IPV p 83, Dec 88
 Precision high-voltage dc regulator
 AG6K p 75, Aug 88
 Quick fix for soldering irons (HN)
 W2YW p 62, Apr 84
 Reflected power limiter
 K4KI p 63, Jul 84
 Remote base/simplex phone patch controller
 AA4NX and KK4LA p 54, Aug 88
 Rewinding transformers with CAD
 W6WTU p 74, Mar 87
 RF filters, Build narrowband
 WB4EHS p 10, Mar 86
 Short circuit p 36, Jun 86
 Silk screen techniques, make your own board using
 W3QOM p 83, Nov 84
 Silverplating, safe, sensible
 K9EYY p 29, Feb 85
 Simple low-cost comb generator frequency calibrator
 Martin, Larry p 78, Jul 88
 Simple receivers from complex ICs
 W6VEH p 10, Nov 88
 Solar power for your ham station
 NH6N p 14, Dec 84
 Structural evaluation of Yagi elements
 K5IU p 29, Dec 88
 Superhet coilset, design with a microcomputer
 Sterrenburg, FAS p 113, Nov 84
 The Guerri report: pc boards
 W6MGI p 109, Sep 86
 Tuning indicator for RTTY and packet radio
 W0HZR p 65, Sept 88
 Two in one: trace doubler for CRO, and square wave and pulse generator (HN)
 Tseng Liao p 26, Dec 88
 2-meter monitor
 WA3ENK p 64, Jul 88
 Universal analog breadboard, A
 Gruchella, Michael p 85, Jun 86
 ZX-81/TS1000 controller: new use for old computers
 N9NB p 31, Dec 86

DIGITAL TECHNIQUES

Add a digital readout to the "poor man's spectrum analyzer"
 WA2PZO p 84, Sept 88
 Amateur FSK: A spectral analysis
 WA6NCX p 42 Dec 86
 AMTOR, AX 25, and HERMES: a performance analysis of three systems
 W9JD p 63, Dec 85

Comments, G3PLX p 9, May 86
 Annunciator bell for the Kantronics
 KPC-2
 K1ZJH p 22, Aug 86
 Audio filter design, computer-aided
 KE2J p 15, Oct 85
 AUTOTRAK, simple rotor interface board for the C-64, VIC-20 and applicable to other popular computers
 K7NH p 10, Dec 87
 Build a QSO "beeper"
 KF6CU p 38, Jan 88
 CAT control system for the Yaesu
 FT-757GX
 SM6CPI p 26, Nov 87
 Commodore 64, \$100 printer (HN)
 W2QLI p 86, Aug 85
 Computer control of ICOM R-71, 271, 471, and 751 radios
 NG6Q p 47, Apr 86
 Comments: Continuous phase tones
 G3VMR p 6, Aug 87
 Decoding data signals
 WB4GCS p 60, Dec 88
 Deluxe logic probe
 MWilde p 74, Jan 87
 Digital can do more, Comments
 KA4JFO p 9, Mar 86
 Digital clock, build a fail-safe
 K1MC p 54, Oct 85
 Digital frequency readout using the Commodore 64
 W3NNL p 83, Nov 85
 Digital HF radio: a sampling of techniques
 KA2WEU/DJ2LR p 19, Apr 85
 Short circuit p 121, May 85
 Direct synthesis VFO
 W7SX p 10, Sept 88
 DTMF controller for repeaters
 WB4FXD p 47, Sep 85
 DTMF tone signaling circuit
 WV6A p 42, Sept 88
 Elmer's notebook: An introduction to digital communications
 W1SL p 92, Jul 87
 Elmer's notebook: An introduction to AMTOR
 W1SL p 101, Sept 87
 Elmer's notebook: packet radio
 W1SL p 100, Oct 87
 Frequency synthesis up to 2 GHz
 WA6DYW p 22, Apr 88
 Get on SSTV-with the C-64
 I2CAB and I2AED, edited by K9EI
 p 43, Oct 86
 p 97, Oct 87
 Short Circuit
 HP-IL serial loop
 Martin, Vaughn D p 101, Apr 84
 Improving the WB3CEH programmable call sign identifier (hn)
 KL7XO p 82, Sept 87
 Comments: Packet board update
 VE3LNY p 6, Jan 87
 Packet radio and area networking
 WB3JZO p 38, Dec 84
 Packet radio, automatic frequency and deviation tester
 WB2OSZ p 41, Dec 85
 Packet radio primer
 WA1FHB p 30, Dec 85
 Packet radio: the software approach
 W4UCH p 63, Sep 84
 Packet radio TNC for the IBM PC
 VE3LNY p 10, Aug 86
 PL tone generator, a programmable
 WB0VSZ p 51, Apr 84
 Short circuit p 125, May 84
 Practically speaking: using the digital frequency counter-some pitfalls
 K4IPV p 47, Apr 88
 RAM drive for packet radio
 AD1B p 44, Dec 87
 RTTY reader, interrupt-driven
 KN4L p 72, Sep 84
 Run RTTY on your Timex
 NU4V p 110, Apr 85
 Run RTTY on your VIC-20
 W5TRS p 120, Apr 85
 Satellite tracker, digitally-controlled
 KA8OBL p 102, Sep 85
 Smith Chart impedance matching on your Commodore 64
 WA9GFR p 120, Oct 84
 Software piracy (letter)
 Forsyth, Mike p 8, Sep 84
 Spread spectrum and digital communication techniques: a primer
 N9NB p 13, Dec 85
 The Guerri report computer technology
 W6MGI p 54, Nov 84
 Short circuit p 8, Dec 84
 The Guerri report: signal processing
 W6MGI p 156, Dec 84

The Guerri report
 W6MGI p 124, Jan 86
 The Guerri report
 W6MGI p 125, Apr 86
 Thumbwheel frequency selector for the
 Yaesu FT-757GX
 KA9SNF p 33, Nov 87
 True frequency digital readout for the
 HW-101. A
 NU4F p 8, Jan 87
 Short circuit: p 41, Aug 87
 Using an RTTY termi????h the Heathkit
 HD 4040 TNC
 AA8V p 59, Aug 86
 VIC-20 printer (HN)
 W2QLI p 88, Sep 84

FEATURES AND FICTION

Electromagnetic jargon generator, state-of-the-art
 N6TX p 75, Apr 85
 Ham radio techniques: Ever work a W10
 W6SAI p 43, Feb 87
 Short circuit: p 50, Apr 87
 Ham radio techniques: Xingiang
 Province the last frontier
 W6SAI p 55, Apr 87
 Ham Radio techniques: the year was
 1923...
 W6SAI p 89, Jan 88
 Ham Radio techniques: "the greatest little magazine in the world"
 W6SAI p 68, Feb 88
 One hundred years of electric waves
 KR6A p 22, Aug 88
 Radio addiction: case history of an enthusiast
 W7SX p 52, Jan 88
 Reflections: Returning the spectrum to chaos...courtesy of the FCC (General docket 87-389)
 W9JUV p 6, Feb 88
 Reflections: Novice enhancement and the future of amateur radiod
 W9JUV p 6, Jun 88

FILTERS

Simple VHF/UHF multiple quarter-wave filters
 WA3EWT p 37, Sept 87
 Automatically switched half-octave filters: part 1
 WB3JZO and Watkins, Lee R. p 10, Feb 88
 Automatically switched half-octave filters: part 2
 WB3JZO and Watkins, Lee R. p 29, Mar 88
 Top-down filter design
 VE5FP p 41, Jan 87

FM AND REPEATERS

DTMF controller for repeaters
 WB4FXD p 47, Sep 85
 FM advantage
 WA9GDZ6 p 38, Sep 84
 FM repeater separation 20 kHz. Yes, 15 kHz, No
 WD5IBS p 12, Aug 85
 Improved repeater/transmitter noise performance (HN)
 K1ZJH p 104, Apr 86
 Remote repeater programming using a computer and a telephone
 KD9BC p 89, Mar 86
 Repeater, high-tech: designing and building an FM translator
 WA6CAY p 82, Feb 85
 Repeaters, speech synthesis for
 N9EE p 79, Mar 84
 Repeaters, three circuits for (HN)
 N9EE p 91, Jan 84
 Short circuit p 10, Feb 84
 Short circuit p 10, Mar 84
 Tone burst generator for European repeaters, A
 WA3ECC p 88, Jul 86
 ZIA connection: a multi-state 2-meter repeater link
 K5XY p 30, Oct 86

HAZARDS

AC line transient protection
 N6JH p 59, Apr 86
 Electric shock, the effects and treatment of
 NY6U p 85, Mar 84

INTEGRATED CIRCUITS

Low-pass filter, integrated circuit
 WB2KTG p 59, Jan 85
 Static electricity and modern integrated circuits
 K4KEF p 33, Mar 84
 The Guerri Report: superchips come of age
 W6MGI p 126, Feb 85
 The Guerri report:
 W6MGI p 124, Jan 86
 The Guerri report: microchips
 W6MGI p 109, Jul 86

KEYING AND CONTROL

Call sign identifier: programmable
 WB3CEH p 33, Feb 85
 Ham radio techniques
 W6SAI p 106, Oct 84
 Improving the WB3CEH programmable call sign identifier
 KL7XO p 82, Sept 87
 Keyer, simple, compact QRP (weekender)
 W5FG p 82, Oct 84
 Micros and VHF beacons transmit messages automatically
 K9EI p 51, Jul 85
 Morse Code tutor
 N3SE p 45, Jun 85
 Morse keyboard, an easier approach to mastering the
 W1KZ p 80, Apr 84
 Remotely controlled stations: a look at a successful remote base
 WA6EJO p 48, Sep 86

MEASUREMENTS AND TEST EQUIPMENT

Add a digital readout to the "poor man's spectrum analyzer"
 WA2PZO p 84, Sept 88
 An i-f sweep generator
 W2ZUC p 101, Jan 87
 An rf voltmeter
 G4COL p 65, Nov 87
 Bridge measurements, the half-wave transmission line in (HN)
 K4KI p 108, Nov 84
 Build this simple L-C checker
 W5FG p 19, Dec 88
 Calibrating series-resistance capacitance bridges (HN)
 Caron p 27, Dec 88
 Continuity tester, simple
 WD6GMB p 130, Sep 85
 Deluxe logic probe, A
 M. Wilde p 74, Jan 87
 Detailed look at probes
 Martin, and Davis p 75, Sep 85
 Detector, logarithmic, wideband
 PA0CX/DJ6SA p 75, Jul 85
 Dual wattmeter, 50-500 MHz
 WB4EHS p 67, Jul 85
 Elmer's notebook: power measurements
 W1SL p 100, Jan 88
 Elmer's notebook: standing wave ratio-what does it mean?
 W1SL p 98, Feb 88
 EM/RFI shielding: new techniques part 1
 Martin, Vaughn D. p 72, Jan 84
 EM/RFI shielding: new techniques part 2
 Martin, Vaughn D. p 85, Feb 84
 Extended-range VU meter
 WB6JNN p 59, Sep 86

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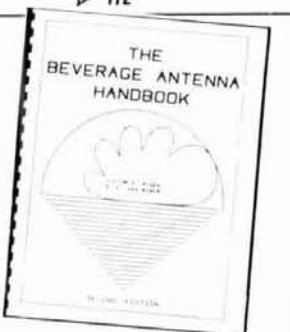
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WWVB
W4ZPS p 45, Mar 88

Frequency counter, "smart"
WASVQK p 41, Oct 84
Short circuit p 126, Apr 85

Frequency and level standard
PA0CX p 10, Jan 86
Comments, WA8LLY p 9, Jun 86

Ground rod resistance
K4MT p 95, Jul 84
Comments p 8, Sep 84

Ham radio techniques: time and frequency station WWVS
W6SAI p 37, Jun 87

High-frequency receiver performance
G4OBU p 33, Feb 84

HP-1B greatly simplified
Martin, Vaughn D. p 65, Mar 84

IF sweep generator, compact
PA0CX/DJ0SA p 35, Jun 85

L and C measurements
WB6ZLN p 117, Oct 84

Low-cost spectrum analyzer with Kilo-buck features
W4UCH p 82, Sep 86

Measuring noise figure
K2BLA p 26, Jan 84

Microphone calibration
NY6U p 73, Jun 84

Multi-featured function generator
WA7IRY p 9 Apr 88

NBS time and frequency survey
NBS p 45, Jun 87

Ode to older oscilloscopes
KR6A p 69, Jan 88

Ohmmeter, wide-range
Bailey, John T p 53, Jan 84

Practically speaking
K4IPV p 79, Dec 85

Practically speaking: using the right multimeter
K4IPV p 95, Jun 86

Practically speaking: using the multimeter
K4IPV p 43, Jul 86

Practically speaking: using antenna noise bridge
K4IPV p 69, May 86

Practically speaking: function generator circuits-part 2
K4IPV p 89, Jan 87

Practically speaking: testing diodes
K4IPV p 65, Feb 87

Practically speaking: building "the poor man's spectrum analyzer"
K4IPV p 99, Mar 87

Practically speaking: build your own time-domain reflectometer
K4IPV p 69, Jun 87

Practically speaking: revisiting "the poor man's spectrum analyzer"
K4IPV p 49, Sep 87

Practically speaking: troubleshooting dc power supplies with an oscilloscope
K4IPV p 57, Oct 87

Practically speaking: using voltage comparators
K4IPV p 49, Nov 87

Practically speaking: generating low-*i*-f frequencies
K4IPV p 49, Dec 87

Practically speaking: using the digital frequency counter-some pitfalls
K4IPV-0 p 47, Apr 88

QRP wattmeter (HN)
W6XM p 110, Jul 84

Receiver sweep alignment system
WB6BIH p 124, Nov 84

Reflected power limiter
K4KI p 63, Jul 84

Sensitive LF or HF field-strength meter
K1RGO p 67, Sep 86

Simple low-cost comb generator frequency calibrator
Martin, Larry p 78 Jul 88

Test DBMs for diode leakage
WB6BIH p 86, Jun 87

The Guerri report: signal processing
W6MGI p 156, Dec 84

Transmitter tuning aid: buffer your load with this resistive network (weekender)
K4KI p 52, Feb 84
Comments, K4KI p 11, Jan 84

Tuneup, safe, silent
K4KI p 123, Dec 84

Two in one: Trace doubler for CRO, and square wave and pulse generator (HN)
Tseng Liao p 26, Dec 88

Two-tone signal generator
YB9ATA/WA7AQN p 25, Feb 86
Short circuit p 45, Apr 86
Short circuit p 36, Jun 86

23 GHz prescaler
N6JH p 21, Jan 87

Understanding noise figure
Gruchalla, M. p 89, Apr 87

VHF noise bridge, a
OE2APM/AA3K p 10, Jul 86

VHF/UHF world
W1JR p 55, Oct 84

SWR bridges
K2LB p 37, Mar 86

Wide-range RF power meter
KA8OBL p 24, Apr 86

MISCELLANEOUS TECHNICAL

ALC circuits, improving amplifier: part 1
WA8AJN p 40, Aug 84

ALC circuits, improving amplifier: part 2
WA8AJN p 38, Sep 84

Amateur FSK: A spectral analysis
WA6NCX p 42, Dec 86

Audio to microwave amplifier, build your own
Gruchalla, Michael p 12, Mar 84
Bicycle-powered station
W1BG p 25, Dec 84

Branch-line hybrid: part 1
WA2EWT p 107, Apr 84

Branch-line hybrid: part 2
WA2EWT p 93, May 84

Broadband amplifier-attenuator
W7SX p 59, Jul 86

Build a 1-1000 MHz amplifier using
MAR-4 MMICs
WB6BIH p 33, Jul 87

Build a QSO "beeper"
KF6CU p 38, Jan 88

Buying topo maps, Comments:
K3SKE p 9, Dec 86

Can I patent it?
K2LZ p 8, Mar 87
Comments: changing fundamental constants of science
W4SXX p 6, Oct 87

Communicating on 474,083 GHz (light wave communications)
WA6EJO p 10, Dec 86

Decibel, defining the
Gruchalla, M. p 51, Feb 85

Electromagnetic interference and the digital era
K3PUR p 114, Sep 84

Elmer's notebook: The mysterious "Q"
W1SL p 110, Sept 88

EMIRFI shielding: new techniques part 1
Martin, Vaughn D. p 72, Jan 84

EMIRFI shielding: new techniques part 2
Martin, Vaughn D. p 84, Feb 84

Filter design, graphic
W6NRW p 37, Apr 84
Short circuit p 13, Jul 84

Function Generator: circuits from your signal generator-part 1
K4IPV p 67, Dec 86

Ham Radio techniques
W6SAI p 63, May 84

Ham Radio techniques, fifty years ago
W6SAI p 58, Jun 84

Ham Radio techniques
W6SAI p 106, Oct 84

Ham Radio techniques
W6SAI p 75, Jan 85

Ham Radio techniques
W6SAI p 59, Feb 85

Ham Radio techniques
W6SAI p 83, Mar 85

Ham Radio techniques: electron-hole theory exposed as fraud
W6SAI p 67, Apr 85

Ham Radio techniques
W6SAI p 66, May 85

Ham Radio techniques
W6SAI p 51, Jun 85

Ham Radio techniques
W6SAI p 59, Jul 85

Ham Radio techniques
W6SAI p 90, Aug 85

Ham Radio techniques: I have seen the future and it works
W6SAI p 91, Sep 85

Ham Radio techniques
W6SAI p 75, Oct 85

Ham Radio techniques
W6SAI p 67, Nov 85

Ham Radio techniques: 9CXX revisited
W6SAI p 83, Dec 87

Ham Radio techniques: line voltage and power tube life
W6SAI p 60, Jul 88

Ham Radio techniques: the joys of TVI or, were you on the air last night?
W6SAI p 70, Aug 88

Harmonics, Trapping stubborn
N1RC p 99, Jan 86

Impedance matching: a brief review
WD4C p 49, Jun 84

Intermittent reception due to lightning (HN)
W2YW p 39, Sep 88

Lightning location and detection
VY1CW p 25, Sep 87

Linear amplifier, 3CX800A7
K8RA p 17, Aug 84

Low-pass filter, integrated circuit
WB2KTG p 59, Jan 85

Mobile theft deterrent: The Weekender
W6WTU p81, Feb 87

Modifying the Trio-Kenwood TS930S
WB9BXT p 67, Apr 86

Monolithic RF amplifiers
N6JH p 22, Mar 86

NE5205 wideband RF amplifier
Gruchalla, Michael p 30, Sep 86
Short circuit: p 72, Jan 87

Neutralizing 572B final at 1500 watts output (HN)
W2YW p 63, Jun 84

New uses for old tuners
W6WTU p 25, Jan 88

Noise cancellation circuit
K1RGO p 75, Mar 84

Peaked lowpass: a look at the ultraspherical filter
W7ZOI p 96, Jun 84

Phase modulator, PLL (HN)
VE3FHM p 117, Jun 85
Comments, K6KVX, Sample Martin, WD8AHO, WB4APT p 10, Feb 84

Polymer film transforms mechanical energy to electrical energy
WA4KFZ p 55, Dec 84

Power FETs: trend for VHF amplifiers
Peters, Daniel, and W7PUA p 12, Jan 84

Power speaker enhances mobile operation (weekender)
K1ZJH p 83, Jan 88

Practically speaking: repairing flood damage
K4IPV p 95, Oct 85

Practically speaking: intermittents, pt. 1
K4IPV p 75, Nov 85

Practically speaking: intermittents, pt. 2
K4IPV p 79, Dec 85

Practically speaking: battery problems, pt. 1
K4IPV p 62, Jul 87

Practically speaking: feedback
K4IPV p 60, May 88

Practically speaking: Overview of op amps-part 1
K4IPV p 100, Nov 88

Practically speaking: overview of op amps-part 2
K4IPV p 83, Dec 88

Prerecorded messages help the hearing impaired (HN)
W2QLI p 87, Sep 84

Quartz crystal resonators
Boddaert, Peter p 85, Feb 86

Remedy for RFI (comment)
K6WX p 9, Jul 88

Resonant circuits
WD4C p 12, Apr 84

RFI filters, Build narrowband
WB4EHS p 10, Mar 86
Short circuit p 36, Jun 86

RFI, solving the problems of
W2YW p 124, Sep 84

Russian Woodpecker, the: a continuing nuisance
KR7L p 37, Nov 84

Solar power for your ham station
NH6N p 14, Dec 84
Short circuit p 145, Mar 85

The Guerri report computer technology
W6MGI p 54, Nov 84
Short circuit p 8, Dec 84

The Guerri report
W6MGI p 124, Jan 85

The Guerri report: superchips come of age
W6MGI p 126, Feb 85

The Guerri report
W6MGI p 158, Mar 85

The Guerri report
W6MGI p 157, Apr 85

The Guerri report: a busy signal from space
W6MGI p 165, May 85

The Guerri report predicting equipment failure
W6MGI p 125, Jun 85

The Guerri report
W6MGI p 124, Jul 85

The Guerri report
W6MGI p 124, Aug 85

The Guerri report: RF power supplies achieve high efficiency
W6MGI p 157, Sep 85

The Guerri report: RF effects the good and the bad
W6MGI p 142, Oct 85

The Guerri report
W6MGI p 140, Nov 85

Two-tone signal generator
YB9ATA/WA7AQN p 25, Feb 86
Short circuit p 45, Apr 86
Short circuit p 36, Jun 86
Comments: "Using the Spectrum Monitor"
K16DW p 9, Nov 86

Using CAD to rewind transformers
W6WTU p 83, Dec 86

Using spreadsheet programs
AD1B p 95, Dec 86

Very sensitive LF or HF field-strength meter
K1RGO p 67, Sep 86

VHF/UHF world: the VHF/UHF primer an introduction to filters
W1JR p 112, Aug 84

VHF noise bridge
OE2APM/AA3K p 10, Jul 86

VSWR bridges
K2LB p 37, Mar 86

Wide-range RF power meter
KA8OBL p 24, Apr 86

NOVICE READING

Cheers from down under, Comments:
VK4QA p 9, Dec 86

Ham radio technique
W6SAI p 59, Dec 86

Elmer's notebook: novice enhancement
W1SL p 95, Jun 87
Short circuit p 95, Aug 87

Elmer's notebook: 220 MHz
W1SL p 91, Aug 87

Elmer's notebook: an introduction to AMTOR
W1SL p 101, Sep 87

Elmer's notebook: packet radio
W1SL p 100, Oct 87

Morse code computer tutor
N3SE p 45, Jun 85

New band privileges for Novice operators (letter)
KA0DOE p 15, Sep 85
Comments, W3YBF p 9, Jan 86
Comments, KD0EV p 9, Jan 86
Comments, WD5H p 9, Jun 86

Novice privileges (letter)
WB9IVR p 9, Oct 85

Practically speaking
K4IPV p 79, Dec 85

Radiotelegraph codes: there's not just one
KR6A p 82, Sept 88

Reflections: Novice enhancement and the 220 MHz band
W9JUV p 4, Apr 87

OPERATING

Buying topo maps, Comments:
K3SKE p 9, Dec 86

Carrier complaint (comment)
WD0P p 9, Jul 88

Carrier-operated CW reception limiter
W6NRW p 113, Sep 85
Comments: DARC awards information
K1RH p 6, Jul 87

Elmer's notebook: 220 MHz
W1SL p 91, Aug 87
Short circuit p95, Aug 87

Elmer's notebook: an introduction to AMTOR
W1SL p 101, Sep 87

Elmer's notebook: packet radio
W1SL p 100, Oct 87

Elmer's notebook: "Q" signals
W1SL p 95, Jun 88

Field Day-preparedness or party time? (Backscatter)
W9JUV and N1ACH p 6, Sept 88

Generation gap in Amateur Radio (comment) N3CCW p 94, Aug 88

Ham bands under siege (Backscatter) N1ACH p 4, Oct 88

Ham Radio techniques W6SAI p 58, Sep 84 p 67, Jan 86 p 65, Feb 86 p 63, Mar 86 p 42, Apr 86 p 39, May 86 p 30, Jun 86 p 66, Jul 86 p 43, Aug 86 p 42, Sep 86 p 38, Oct 86 p 73, Nov 86 p 59, Dec 86

Ham Radio techniques: BY0AA revisited W6SAI p 53, Aug 87

Ham Radio techniques: a new country for you W6SAI p 41, Nov 87

Ham Radio techniques: the joys of TVI or, were you on the air last night? W6SAI p 70, Aug 88

Ham Radio techniques: The radio boys in the Pacific, or, working DX for Uncle Sam W6SAI p 26, Nov 88

INUS system (comment) XE1MD p 9, Jan 88

Legal usefulness of Amateur Radio (comment) WA7AQN p 9, Aug 88

Locator field list S5AGM p 74, Jul 87

Locator field list S5AGM p 89, Oct 87

Market survey of amateurs a good idea (comment) W1FB p 9, p 94 Aug 88

More information needed (comment) W3QQM p 9, Sept 88

Operating etiquette (letter) W9MKV p 12, Jul 84

Potential danger (Backscatter) N1ACH p 4, Nov 88

Re-discovering ham radio (comment) KC1JG p 9, Aug 88

Service not hobby (letter) W5VSR p 8, Aug. 85 Comments, KA1YE p 11, Jan 84

TOM remembered (letter) W1ESN p 11, Jan 84 Comments, K4KI p 11, Jan 84

VHF/UHF world: operating a VHF/UHF micro-wave station W1JR p 38, Jul 87 Short circuit p 97, Oct 87

VHF/UHF World: Loose ends W1JR p 53, Sept 88

Volunteer examiners: keep standards high (letter) K6WX p 12, May 84

PL tone generator, a programmable WB0VSZ p 51, Apr 84

Short circuit p 125, May 84

Practically speaking: drift and shift K4IPV p 75, Jan 88

Universal oscillator circuit VE6RF p 38, Apr 86

VCO, 1800-2600 MHz W0DTV p 21, Jul 85

Wideband VCO design WA4MGX p 49, Jul 84

PACKET

Amateur packet radio networking and protocols, part 1 KR3T p 33, Feb 88

Amateur packet radio networking and protocols, part 2 KR3T p 56, Mar 88

Amateur packet radio networking and protocols, part 3 KR3T p 41, Apr 88

C-64 and GLB PK-1 interface circuit W2EHD p 87, Mar 87

Comments: packet board update p 6, Jan 87

Elmer's notebook: packet radio W1SL p 100, Oct 87

Exploring packet radio with KISS WA8BXN p 9, Oct 88

Formatted display of packet using KISS WA8BXN p 51, Dec 88

4800 baud modem for VHF/UHF packet radio VE3DNL, VE3DNM, VE3DVV & VE3LNY p 10, Aug 88

Packetimer for the PK-1 W2EHD/exW8KGN p 93, Mar 87

Packet radio conference bridge W5HJP p 24, Apr 87

Packet radio PSK modem for JAS-1/F0-12 G3RUH p 8, Feb 87

RAM drive for packet radio AD1B p 44, Dec 87

TEXNET packet-switching network-pt 1 system definition and design WBS5PUC & N5EG p 29, Mar 87

TEXNET packet-switching network-pt 2 hardware design WBS5PUC & N5EG p29, Apr 87

TEXNET packet-switching network-pt 3 software overview WBS5PUC & N5EG p53, Jun 87

Using macros with packet (HN) AD1B p 82, Oct 88

POWER SUPPLIES

An easy-to-build NiCd pulse charger (weekender) AG6K p 18, Sept 88

Battery-backed master power system K9ES p 17, Jan 88

Battery charger, NiCd, constant current, a pulsed K2MWU p 67, Aug 85

Battery storage (comment) W5JHJ p 6, May 88

Get the most from your NiCds (Weekender) K3OF p 88, Dec 88

Low-voltage power supplies, designing W4MLE p 46, Mar 85

Short Circuit p 121, May 85

Precision high-voltage dc regulator AG6K p 75, Aug 88

Power supply, six-output Martin, Vaughn D p 12, Oct 84

Power supply, switching high-voltage W5FG p 48, Apr 84

Practically speaking: bench power supply K4IPV p 55, Mar 86

Practically speaking: battery problems pt 1 K4IPV p 62, Jul 87

Practically speaking: battery problems pt 2 K4IPV p 73, Aug 87

Pulse width modulated dc-to-dc converters W3CZ p 65, Oct 87

Regulated screen grid power supply, A AG6K p 51, Jun 86

Storing lead-acid batteries (comment) N5OP p 9, Sept 88

Batteries on concrete (comment) N5OP p 101, Sept 88

Temperature control, automatic WB5IRI p 75, Jun 85

The Guerri report: RF power supplies achieve high efficiency W6MGI p 157, Sep 85

Transformers, wind your own inexpensively W4GDW p 96, Jun 85

PROPAGATION

Achieve polarization diversity through variable power splitting W3NGJ p 10, Feb 88

DX forecaster p 83, Jan 84 p 79, Feb 84 p 93, Mar 84 p 93, Apr 84 p 119, May 84 p 109, Jun 84 p 103, Jul 84 p 63, Aug 84 p 79, Sep 84 p 100, Oct 84 p 92, Nov 84 p 63, Dec 84 p 94, Jan 85 p 75, Feb 85 p 117, Jun 85 p 120, Mar 85 p 84, Apr 85 p 79, May 85 p 102, Jun 85 p 100, Jul 85 p 100, Aug 85 p 122, Sep 85 p 105, Oct 85 p 92, Nov 85 p 112, Jan 86 p 78, Feb 86 p 97, Mar 86 p 99, Apr 86 p 118, May 86 p 101, Jun 86 p 91, Jul 86 p 90, Aug 86 p 98, Sep 86 p 92, Oct 86 p 84, Nov 86

Short circuit: HORANT program, p 92, Oct 86 p 9, Nov 86 p 84, Dec 86

DX forecaster: Winter anomalous absorption K0RYW p 101, Dec 86

DX forecaster: DX propagation K0RYW p 108, Jan 87

Comment: HORANT for CP/M K4GIO p 6, Feb 87

DX forecaster: more DX propagation tips p 88, Feb 87

DX forecaster: equinox problems p 106, Mar 87

DX forecaster: a spring DX solution p 97, Apr 87

DX forecaster: 1986 propagation review p 105, May 87

DX forecaster: sporadic-E season p 66, Jun 87

DX forecaster: summer thunderstorm noise p78, Jul 87

DX forecaster: summertime DX p 82, Aug 87

DX forecaster: more sporadic-E p 85, Sep 87

DX forecaster: equinox season DX K0RYW p 85, Oct 87

DX forecaster: winter DX K0RYW p 57, Nov 87

DX forecaster: dxing via the winter anomaly K0RYW p 91, Oct 87

Comments: low band DXing W0SII p 6, Apr 87

Dx forecaster: solar cycle update K0RYW p 96, Jan 88

DX forecaster: transequatorial DX update K0RYW p 90, Feb 88

JX forecaster: the ultimate antipode DX K0RYW p 78, Mar 88

JX forecaster: DX signal quality K0RYW p 80, Apr 88

DX forecaster: 1987 propagation summary K0RYW p 92, May 88

DX forecaster: sporadic E season-1988 K0RYW p 88, Jun 88

DX forecaster: summer thunderstorm noise K0RYW p 83, Jul 88

DX forecaster: summer signal levels K0RYW p 88, Aug 88

DX forecaster: high sunspot propagation problems K0RYW p 104, Sept 88

DX forecaster: high sunspot propagation problems-part 2 K0RYW p 96, Oct 88

DX forecaster: Winter DX season K0RYW p 108, Nov 88

DX forecaster: Winter DX anomalies K0RYW p 110, Dec 88

Dxing by computer NS6N and Buchanan, Walter p 81, Aug 84

Elmer's notebook: propagation basics W1SL p 81, Aug 88

EME link calculator program KE6ZE p 9, Feb 86

Comments, KC8OH p 70, Apr 86

Grayline propagation, fundamentals of KR7L p 77, Aug 84

Ham Radio techniques: Dx is getting better and better! Here's why! W6SAI p 28, Apr 88

Ham Radio techniques: On our way up! W6SAI p 26, Sept 88

Ham Radio techniques: New Zealand, Maui, and the solar cycle W6SAI p 22, Dec 88

HF ground wave propagation WA9GFR p 81, May 86

How to plot great circles on your favorite map W4BW p 81, Aug 86

L-band ground wave propagation program WA9GFR and Joseph R Hennel p 103, Jan 86

Comment, WA9GFR p 9, Apr 86

Moon coordinates, determining basic W2WD p 38, Jan 85

Moon-tracking by computer K6WX p 38, Mar 84

New band propagation KK2XJM (W4MB) p 12, Jan 83

Pathfinder—part two K3FR p 47, Oct 88

Radio astronomy and the search for extra terrestrial intelligence WB3JZO p 10, Mar 85

Return to the 360-degree propagation prediction N4UJH p 41, Oct 87

Russian Woodpecker, the: a continuing nuisance KR7L p 37, Nov 84

Solar activity and the earth's magnetosphere KR7L p 8, Aug 87

Solar outages, predicting VE7ABK p 75, Mar 85

Sporadic E and 50-MHz transatlantic propagation during 1987 G3NAQ p 10, Jul 88

360-degree MINIMUF propagation prediction N4UJH p 25, Feb 87

VHF meteor scatter communications A17J p 69, Feb 84

VHF/UHF world: improving meteor scatter communications W1JR p 82, Jun 84

VHF/UHF world: the VHF/UHF Primer, an introduction to propagation W1JR p 14, Jul 84

VHF/UHF world W1JR p 45, Sep 84

VHF/UHF World: propagation update W1JR p 86, Jul 85

VHF/UHF World W1JR p 85, Dec 85

VHF/UHF world: meteor scatter communications W1JR p 68, Jun 86

Short circuit p 87, Jul 86

VHF/UHF world: μ W and mm-wave propagation: part 2 W1JR p 69, Aug 86

VHF/UHF world: propagation update-part 2 W1JR p 39, Jun 88

VHF/UHF world: propagation update-part 3 W1JR p 38, Jul 88

OSCILLATORS

Audio oscillator to pulse generator conversion (HN) W0DLQ p 50, Oct 84

Better frequency stability for the Drake TR7 HB9ABO p 21, Aug 87

Direct synthesis VFO W7SX p 10, Sept 88

Frequency synthesis by VXO harmonic selection W3MT p 12, Feb 84

Frequency synthesis up to 2 GHz WA6DYW p 33, Apr 88

High-stability BFO for receiver applications K1ZJH p 28, Jun 85

Local oscillators, high stability for micro-wave receivers and other applications WB3JZO p 29, Nov 85

Low-noise phase-locked UHF VFO part 1: the noise problem WA9HUV p 33, Jul 86

Short circuit: Low-noise UHF VFO WA9HUV p 9, Dec 86

Low-noise phase-locked UHF VCO part 2: construction and testing WA9HUV p 25, Aug 86

Oscillator, voltage controlled, uses ceramic resonators K2BLA p 18, Jun 85

Short Circuit p 27, Aug 85

RECEIVERS AND CONVERTERS

general

Cascaded stages, IMD and intercept points of
W3IMG p 28, Nov 84
CB to 10-meter conversions, scanner
W2FMY, KB2GA p 98, Nov 85
Compact 75-meter monoband transceiver
K1BQT p 13, Nov 85
Short circuit p 66, Jan 86
Digital frequency readout using the Commodore 64
W3NNL p 83, Nov 85
Elmer's notebook: receiver buzzwords
W1SL p 100, Nov 87
Extending receive coverage for the IC-02 and IC-04
WB6GTM p 77, Jul 86
External product detector improves receiver performance
W6GB p 107, Nov 85
Frequency calibration using 60 kHz
WVVB p 45, Mar 88
W4ZPS p 45, Mar 88
Ham radio techniques: "white noise" technology bites back
W6SAI p 55, Jan 87
Ham radio techniques: "white noise" revisited
W6SAI p 79, Oct 87
High dynamic range mixing with the Si 8901
KB6QJ p 11, Mar 88
High-stability BFO for receiver applications
K1ZJH p 28, Jun 85
Mixer frequencies, graphical selection
W2HVN p 41, Jun 85
Noise discriminator, a pulsewidth
W6NRW p 23, Nov 84
Noise, understanding and handling
DJ2LR p 10, Nov 86
Preamp at work, Quiet!
N6TX p 14, Nov 84
Receiver input temperature (letter)
W6JTD p 13, Apr 85
Receiver tuning mechanism selection
PY2PEIC p 31, Nov 86
Receiver, 10 through 80-meter home brew
N1BFV p 40, Nov 85
S-meter, a calibrated
W7SX p 23, Jan 86
Short circuit p 45, Apr 86
Spectrum analyzer, a handheld optical
WA4WDL p 23, Apr 84
Ten-Tec Argosy, Upgrade
WB3JZO p 38, Nov 86
True frequency digital readout for the HW-101
NU4F p 8, Jan 87
Short circuit p 41, Aug 87
TS-930S headset audio, increase undistorted (HN)
W6FR p 128, Oct 85
VHF/UHF world high dynamic range receivers
W1JR p 97, Nov 84
Short circuit p 103, Jan 85
VHF/UHF world: broadband amplifiers in receiver design
W1JR p 91, Nov 86
VHF/UHF World: low-noise receiver update part 1
W1JR p 77, Nov 87

hf

Better frequency stability for the Drake TR7
HB9ABO p 21, Aug 87
CAT control system for the Yaesu FT-757CX
SM6CPI p 26, Nov 87
Comments KA0GPE p 10, Mar 84
Compact 20-meter CW receiver, A
K1BQT p 8, Jun 87
Short circuit: p 6, Jul 87
Short circuit: p 81, Sep 87
Designing a state-of-the-art receiver
KA2WEU/DJ2LR p 11g, Nov 87
Digital HF radio: a sampling of techniques
KA2WEU/DJ2LR p 19, Apr 85

Short circuit p 121, May 85
Frequency calibration using 60 kHz
WVVB
W4ZPS p 45, Mar 88
HF superhet, 20-meter
N3ECZ p 65, Nov 86
High dynamic range mixing with the Si 8901
KB6QJ p 11, Mar 88
High-frequency receiver performance
G4OBU p 33, Feb 84
Pepperdine receiver
W6QIF p 33, Nov 88
Receiver, Pocket-portable SSB
WB6BIH p 55, Nov 86
Receiver sweep alignment system
WB6BIH p 124, Nov 84
Shortwave receiver, portable
PY2PEIC p 67, Apr 84
Simple direct conversion receiver
WA3ENK p 9, Dec 88
Simple receivers from complex ICs
W6VEH p 10, Nov 88
Solid-state 75A-4 receiver
KF7M p 67, Nov 88
Superhet coilset, design with a microcomputer
Sterrenburg, FAS p 113, Nov 84
SW receiver, a double conversion portable
PY2PEIC p 48, Nov 84
Thumbwheel frequency selector for the Yaesu FT-757-GX
KA9SNF p 33, Nov 87
Transceivers, quasi-bilateral if for
K1ZJH p 75, Dec 84
Two-band receiver, extending the modular
WA3TFS p 57, Nov 84
Comments WA3TFS p 8, Sep 84
Tomorrow's receivers: what will the next 20 years bring
W7SX p 8, Nov 87
80-meter receiver, simple
WB2EAV p 25, Nov 86

vhf

Extending receive coverage for the IC-02 and IC-04
WB6GTM p 77, Jul 86
Modular transmit and receive converters for 902 MHz
N6JH p 17, Mar 87
VHF/UHF world: VHF/UHF receivers
W1JR p 42, Mar 84
VHF/UHF World: low noise receiver update-part 1
W1JR p 77, Nov 87
VHF/UHF World: low noise receiver update-part 2
W1JR p 72, Dec 87

RTTY

New MSO for RTTY (letter)
N2EO p 12, Jul 84
Short circuit p 10, Feb 84
RTTY oscilloscope input using line transformers (HN)
W6XM p 87, Sep 84
Run RTTY on your Timex
NU4F p 110, Apr 85
Run RTTY on your VIC-20
W5TRS p 120, Apr 85
Timex/Sinclair newsletter (letter)
AD1B p 12, Jul 84
Tuning indicator for RTTY and packet radio
W0HZR p 65, Sept 88
VIC-20 printer (HN)
W2QLI p 88, Sep 84
Short circuit p 145, Mar 85

SATELLITES

Demodulator, telemetry, PSK, for OS-CAR 10
G3RUH p 50, Apr 85
Elevation indicator, inexpensive
W5JTL p 67, Jun 85
First HT-to-HT QSO via OSCAR 10
WA2LQQ p 32, Sep 84
G.O.E.S. reception: a simple approach
WA4WDL p 46, Jan 84
Introducing satellite communications
G3ZCZ p 10, Apr 86

Moon-tracking by computer
K6WX p 38, Mar 84
Packet radio PSK modem for JAS-1/FO-12
G3RUH p 8, Feb 87
Satellite tracker, digitally-controlled
KA8OBL p 102, Sep 85
Signals from space, receiving
K8UR p 67, Nov 84
The Guerri report: super speed semiconductor
W6MGI p 109, Oct 86
The Guerri report: communication satellites
W6MGI p 108, Jun 86
Comments: update on ACSSB level-one adapter, project OSCAR (Oct 86)
WB6JNN p 99, Nov 86
Work OSCAR 10 with your HT
WA2LQQ p 29, Sep 84

SEMI-CONDUCTORS

Cooling semiconductors part 1: designing and using heatsinks
Martin, Vaughn D p 33, Jul 84
Cooling semiconductors part 2: blowers and fans
Martin, Vaughn D p 52, Aug 84
High dynamic range mixing with the Si 8901
KB6QJ p 11, Mar 88
Practically speaking: solid state rectifiers
K4IPV p 51, Aug 86
Practically speaking: substituting transistors-part 1
K4IPV p 92, Sep 86
Practically speaking: substituting transistors-part 2
K4IPV p 66, Oct 86
Practically speaking: non-ideal linear IC amplifiers
typical problems and how to solve them
K4IPV p 72, Jul 88
The Guerri report: super speed semiconductors
W6MGI p 109, Oct 86
Transistor biasing, back to basics
WD4C p 91, Dec 84
VHF/UHF world: the ubiquitous diode
W1JR p 51, Feb 87
VHF/UHF WORLD: The ubiquitous diode part 2
W1JR p 55, Mar 87

SINGLE SIDEBAND

ACSSB: a level-one adapter
WB6JNN p 10, Oct 86
Adjusting SSB amplifiers
AG6K p 33, Sep 85
Better sounding SSB
AG6K p 58, Feb 84
Comments W2OZH p 13, Jun 84
Development of Amateur SSB: a brief history
K4KJ p 12, Sep 84
Comments, AG4R p 8, Dec 84
Elmer's notebook: power measurements
W1SL p 100, Jan 88
Elmer's notebook: SSB basics-generating the signal
W1SL p 117, Nov 88
Elmer's notebook: SSB basics-receiving the signal
W1SL p 117, Dec 88
Ham radio techniques
W6SAI p 106, Oct 84
Linear amplifier, HF solid-state kilowatt, mobile
WA7SPR p 67, Feb 85
Weaver modulation, 2-meter transmitter
N1COX p 12, Jul 85

SOFTWARE

BASIC program analyzes simple ladder networks
W3NQN p 32, Aug 87
Short circuit p 97, Oct 87
Design a no-tune amplifier with your personal computer
W7DHD p 8, Sep 87

Design program for the grounded-grid
3-500Z
W7DHD p 8, Jun 88
EME link calculator program
KE6ZE p 70, Feb 86
Comments, KC8OH p 9, Apr 86
Get on SSTV-with the C-64
I2CAB and I2AED, edited by K9EI
p 43, Oct 86
Great circle computations using LOTUS 1-2-3
AD1B p 31, Sept 88
L-band ground wave propagation program
WA9GRF and Joseph R. Hennesl
p 103, Jan 86
Morse code teaching tools for the C-64 and 128
KB8CS p 35, Jan 88
Pathfinder: improved MINIMUF program
K3FR p 26, May 88
Pathfinder-part 2
K3FR p 47, Oct 88
Using macros with packet
AD1B p 82, Oct 88
Using spreadsheet programs for amateur radio projects
AD1B p 95, Dec 86

TELEVISION

A tour through an NTSC TV station-part 1 (historical aspects)
KL7AJ p 57, Dec 87
Get on SSTV with the C-64
K9EI p 43, Oct 86
Short Circuit p 97, Oct 87
Remarks on television series (comment)
KB9FO p 6, May 88
Technology of commercial television-part 2: hardware
KL7AJ p 54, Jan 88

TRANSMITTERS AND POWER SUPPLIES

general

Adjusting SSB amplifiers
AG6K p 33, Sep 85
Aural vco provides relative metering
K1ZJH p 97, Jan 87
Design a no-tune amplifier with your personal computer
W7DHD p 8, Sep 87
Grounded-grid amplifier parasitics
AG6K p 31, Apr 86
Comment, NJOG p 9, Jul 86
Comment, W2YW p 6, Jul 86
Ham radio techniques: super cathode driven amplifier
W6SAI p 73, Nov 86
Ham radio techniques: "white noise" technology bites back
W6SAI p 55, Jan 87
Ham radio techniques: "white noise" revisited
W6SAI p 79, Oct 87
MC1496, improved carrier suppression (HN)
K1ZJH p 78, Apr 85
Short circuit p 74, Jul 85
MMIC multiplier chains for the 902 MHz band
N6JH p 72, Feb 87
Short circuit p 64, May 87
Practically speaking: noise, signals and amplifiers
K4IPV p 77, Feb 88
RF switching, high power with pin diodes
KN8Z p 82, Jan 85
Three-tube 4CX250B linear amplifier
YU1AW p 63, Apr 87
True frequency digital readout for the HW-101
NU4F p 8, Jan 87
Short circuit p 41, Aug 87

hf

Amplifier, 3CX1200A7 10 to 80 meter
K8RA p 75, Aug 85
Better frequency stability for the Drake TR7
HB9ABO p 21, Aug 87

CAT control system for the Yaesu FT-757GX SM6CPI p 26, Nov 87

Compact 75-meter monoband transceiver K1BQT p 13, Nov 85

Convert a \$25 CB HT for 6 meters K1ZJH p 79, Aug 87

Design an amplifier around the 3CX1200A7 W7DHD p 33, Dec 87

Ham notebook:curing FT-1012D key clicks N5RM p 74, Feb 88

Ham radio techniques: 160-meter equipment W6SAI p 77, Mar 87

High dynamic range mixing with the Si 8901 KB7QJ p 11, Mar 88

Linear amplifier, HF, solid-state kilowatt, mobile WA7SPR p 67, Feb 85

Thumbwheel frequency selector for the Yaesu FT-757GC KA9SNF p 33, Nov 87

TS-440 interface for keying linears with high voltage biasing (HN) W6WTU p 98, Nov 88

Vacuum tube amplifier, design a toroidal tank circuit for W6YUY p 29, Aug 85

Short circuit p 66, Jan 86

TROUBLE-SHOOTING

GLA-1000 amplifier, stop blowing finals G4CFY, G3RQG p 59, Aug 85

Grounded-grid amplifier parasitics AG6K p 31, Apr 86

Comment, NJ0G p 9, Jul 86

Comment, W2YW p 6, Jul 86

Practically speaking: coax velocity factor K4IPV p 78, Nov 86

Practically speaking: using the multimeter K4IPV p 43, Jul 86

Practically speaking: using the right multimeter K4IPV p 95, Jun 86

Practically speaking K4IPV p 35, Feb 86

Practically speaking K4IPV p 59, Jan 86

TVI problem, solving a difficult (HN) W2YW p 152, Sep 85

VHF AND UHF general

ATV power amplifier, fast-scan WB0ZJP p 67, Mar 85

Audio to microwave amplifier, build your own Gruchalla, Michael p 12, Mar 84

Bandpass filter design, interdigital, computer-aided N6JH, Monemzadeh p 12, Jan 85

Short circuit p 117, Jun 85

Bicycle mobile NH6N p 38, Sept 88

Converting mobile microphones for hand-held VHF transceiver KD8KZ and WB3JCC p 79, Mar 86

Designing a microwave amplifier Domanski, S p 30, Sep 87

Dual wattmeter, 50-500 Hz WB4EHS p 67, Jul 85

Duplexer, six cavity, home-brewed K9EYY p 12, Feb 85

EME link calculator program KE8ZE p 70, Feb 86

Elevation indicator, inexpensive W5JTL p 67, Jun 85

Elmer's notebook: 220 MHz W1SL p91, Aug 87

Elmer's notebook: 1200 MHz band W1SL p 113, Dec 87

Get on 6 meters the inexpensive way KB1KJ p 91, Mar 85

GOES reception: a simple approach WA4WDL p 46, Jan 84

L-band ground wave propagation program WA9GFR and Joseph R Hennel p 103, Jan 86

Local oscillators, high stability for microwave receivers and other applications WB3JZO p 29, Nov 85

Measuring noise figure K2BLA p 26, Jan 84

Micros and VHF beacons transmit messages automatically K9EI p 51, Jul 85

Microstrip impedance program K8UR p 84, Dec 84

MMIC multiplier chains for the 902 MHz band N6JH p 72, Feb 87

Short circuit p 64, May 87

Modular transmit and receive converters for 902 MHz N6JH p 17, Mar 87

Monolithic RF amplifiers N6JH p 22, Mar 86

Moon coordinates, determining basic W2WD p 38, Jan 85

Moon-tracking by computer K6WX p 38, Mar 84

Novice enhancement and the 220 MHz band, Reflections: W9JUV p 4, Apr 87

Power dividers, extended/expanded W5JTL p 73, Oct 84

Power FETs: trend for VHF amplifiers W7PUA and Peters, Dex DL4VJ p 12, Jan 84

Practically speaking: parametric amplifiers K4IPV p 65, Mar 88

Preamp at work, Quiet! N6TX p 14, Nov 84

Remote base/simplex phone patch controller AA4NX & KK4LA p 54, Aug 88

RF transmission cable, microwave applications K3HW p 106, May 85

Silverplating, safe, sensible K9EYY p 29, Feb 85

Simple VHF/UHF multiple quarter-wave filters WA3EWT p 37, Sep 87

Sporadic E and 50-MHz transatlantic propagation during 1987 G3NAO p 10, Jul 88

The Guerri report: signal processing W6MGI p 156, Dec 84

The Guerri report: mm waves, part 1 W6MGI p 109, Feb 86

The Guerri report: mm waves, part 2 W6MGI p 117, Mar 86

The Guerri report: fiber optics W6MGI p 141, May 86

Trade off power for antenna gain at VHF WA9GFR, Hennel p 32, Jul 85

Comment, WA9GFR p 9, Apr 86

23 GHz prescaler N6JH p 21, Jan 87

UHF antenna tower, low-cost KA6GVY p 30, Oct 84

VHF amplifiers, carrier-operated relay WB3JCC, KD8KZ p 45, Apr 85

VHF meteor scatter communications A17J p 69, Feb 84

VHF noise bridge OE2APM/AA3K p 10, Jul 86

VHF signal generation, harmonic mixer K1ZJH p 40, Mar 85

Short circuit p 121, May 85

VHF/UHF world: the VHF/UHF challenge W1JR p 42, Jan 87

VHF/UHF world: improving meteor scatter communications W1JR p 82, Jun 84

VHF/UHF world: microwave bands W1JR p 44, Jan 86

VHF/UHF world: the VHF/UHF primer, an introduction to propagation W1JR p 14, Jul 84

VHF/UHF world: the VHF/UHF Primer, an introduction to filters W1JR p 112, Aug 84

VHF/UHF world W1JR p 45, Sep 84

VHF/UHF world W1JR p 55, Oct 84

VHF/UHF world low-noise GaAs FET technology W1JR p 99, Dec 84

VHF/UHF world: high power amplifiers: part 1 W1JR p 97, Jan 85

VHF/UHF world: high power amplifiers: part 2 W1JR p 38, Feb 85

VHF/UHF world: keeping VHF/UHFers up-to-date W1JR p 126, Mar 85

VHF/UHF world: protecting equipment W1JR p 83, Jun 85

VHF/UHF world: propagation update W1JR p 86, Jul 85

VHF/UHF world: designing and building loop Yagis W1JR p 56, Sep 85

VHF/UHF world transmission lines W1JR p 83, Oct 85

Comment, W9ICZ p 9, Apr 86

VHF/UHF world W1JR p 54, Nov 85

VHF/UHF world W1JR p 85, Dec 85

VHF/UHF world: μ w and mm-wave propagation, part 2 W1JR p 69, Aug 86

VHF/UHF world: meteor scatter communications W1JR p 68, Jun 86

Short circuit p 87, Jul 86

VHF/UHF world: microwave bands W1JR p 44, Jan 86

VHF/UHF world: 33 cm-our newest band W1JR p 83, Apr 86

Short circuit (p 87, July 86) p 9, Aug 86

VHF/UHF world: rf connectors, part 1 W1JR p 77, Sep 86

VHF/UHF world: rf connectors, part 2 W1JR p 59, Oct 86

VHF/UHF world: microwave and millimeter-wave update W1JR p 63, Jan 87

VHF/UHF world: 33 cm update W1JR p 74, Apr 87

Short circuit p 81, Sep 87

VHF/UHF world: microwave portable operation W1JR p 75, Jun 87

Short circuit p 81, Sep 87

VHF/UHF world: minimum requirements for 2-meter EME-pt 2 W1JR p 65, Sep 87

VHF/UHF world: Operating a VHF/UHF microwave station W1JR p 38, Jul 87

Short circuit p 81, Sep 87

Short circuit p 97, Oct 87

VHF/UHF world: minimum requirements for 2-meter EME-pt 1 W1JR p39, Aug 87

Comments, W7WRQ p 9, Dec 87

VHF/UHF World: impedance matching techniques W1JR p 27, Oct 87

VHF/UHF world: loose ends W1JR p 82, Feb 88

VHF/UHF world: power splitters and summers W1JR p 80, May 88

VHF/UHF world: IMD and splatter W1JR p 71, Oct 88

23 GHz prescaler N6JH p 21, Jan 87

antennas

Antenna insulators, PTFE VHF W5JTL p 98, Oct 85

Cheap and dirty 6-meter beam W5UOJ p 56, Jul 88

Convert an inexpensive CB mag-mount antenna into a superb 2-meter whip K7DBA p 52, Oct 86

Colagi antenna, The VE3BFM p 61, May 86

Computer-aided design of long VHF Yagi antennas VK4ZF p 28, May 86

Cylindrical feedhorns revisited WA9HU p 20, Feb 86

Direction-finding tool, the fox box K1ZJH p 25, Oct 85

Ham notebook: 2-meter halo antenna NRS5A p 63, May 87

High-performance Yagis for 432 MHz K1FO p 8, Jul 87

Comments: KLM balun Scott, W p 6, Sep 87

Short circuit p 97, Oct 87

Long 2-meter collinears a simple way to achieve gain (HN) WB3AYW p 95, May 86

Open-wire line for 2-meters N4UH p 94, Jan 87

VHF/UHF world: VHF/UHF antennas and antenna systems W1JR p 46, Feb 84

Short circuit p 54, Jan 86

VHF/UHF world: stacking antennas, part 1 W1JR p 129, Apr 85

VHF/UHF world: stacking antennas, part 2 W1JR p 95, May 85

VHF/UHF world W1JR p 85, Dec 85

VHF Yagi CAD on the C-64 W4PFZ p 70, Sep 86

VHF/UHF world: Yagi facts and fallacies W1JR p 103, May 86

VHF/UHF world: reflector antennas, part 1 W1JR p 51, Feb 86

Short circuit p 45, Apr 86

VHF/UHF world: reflector antennas, part 2 W1JR p 68, Mar 86

Yagi, a high-gain 70-cm W1JR p 75, Dec 86

Short circuit p 49, Jul 87

VHF/UHF world: Optimized 2- and 6-meter Yagi W1JR p92, May 87

Short circuit p 26, Jun 87

Short circuit p 41, Aug 87

Short circuit p 81, Sep 87

Yagi trigon reflector, Optimizing WB3BGU p 84, Jan 86

2-meter beam, portable KB5QJ p 113, Oct 85

6-meter kilowatt amplifier KX00 p 50, Jul 86

receivers and converters

Local oscillators, high stability for microwave receivers and other applications WB3JZO p 29, Nov 85

TR-2500/2600 2-channel programming (HN) K9MLD p 128, Oct 85

VHF/UHF world: VHF/UHF receivers W1JR p 42, Mar 84

VHF/UHF world low-noise GaAs FET technology W1JR p 99, Dec 84

VHF/UHF world W1JR p 54, Nov 85

VHF/UHF World: low noise update, part 2 W1JR p 72, Dec 87

Yaesu's latest VHF/UHF receiver, add general coverage W6MGI p 67, Oct 85

Short circuit p 97, Oct 87

2-meter monitor WA3ENK p 64, Jul 88

1296-MHz low noise amplifier (Weekender) WA9HUV p 60, Nov 88

transmitters

Amplifier, 432-MHz, 1500-watt W2GN p 40, Jul 85

Low-noise phase-locked UHF VCO part 1: the noise problem WA9HUV p 33, Jul 86

Short circuit p 9, Dec 86

Low-noise phase-locked UHF VCO part 2: construction and testing WA9HUV p 25, Aug 86

Temperature control, automatic WB5IRI p 75, Jun 85

TR-2500/2600 2-channel programming (HN) K9MLD p 128, Oct 85

VCO, 1800-2600 MHz W00TV p 21, Jul 85

VHF/UHF world: medium power amplifiers W1JR p 39, Aug 85

VHF/UHF world: VHF/UHF exciters W1JR p 84, Apr 84

Short circuit p 60, Oct 84

Weaver modulation, 2-meter transmitter N1COX p 12, Jul 85

X-band beacons WA6EJO p 29, Jan 87

microwave techniques

Designing a station for the microwave bands: part 1 N6GN p 41, Feb 88

Designing a station for the microwave bands: part 2 N6GN p 19, Jun 88

Short circuit: p 35, Oct 88

Designing a station for the microwave bands: part 3 N6GN p 17, Oct 88

Radial line stub design N1BEP p 65, Feb 88

VHF/UHF world: microwave components and terminology-part 1 W1JR p 71, Mar 88

VHF/UHF world: microwave components and terminology-part 2 W1JR p 67, Apr 88

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(continued from page 70)

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900-MHz phase lock loop synthesizer

RF PROTOTYPE SYSTEMS adds the PLL1 to its QUICK BOARD product line. The board is the basis for a 900-MHz Phase-lock Loop Synthesizer. Several PLL configurations can be implemented with user selected divide ratios, VCO, loop filter, and associated components to be installed in the PLL1. The PLL1 lets you build a PLL that allows you to optimize parameters, or produce a low cost frequency source.

The design is based on the Motorola MC145152 dual-modulus, parallel-interface synthesizer IC and uses common dividers and op amps. The loop filter is laid out for a standard third order type 2 PLL. Frequencies are programmed with parallel data input provided by on-board dip switches.

The PLL1 includes a circuit board, schematic, assembly drawing, and an application note on how to build a PLL using the PLL1 QUICK BOARD.

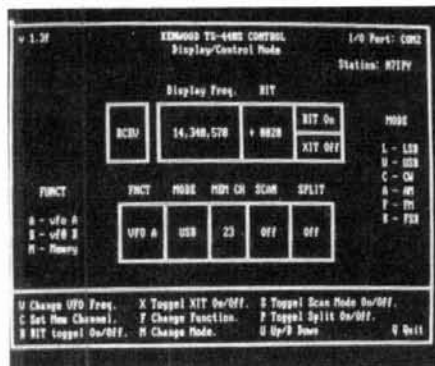
The price in quantities of 1-9 is \$95.00.

For more information, please contact RF PROTOTYPE SYSTEMS, (619) 538-6771, 12730 Kestrel Street, San Diego, California 92129.

Circle #307 on Reader Service Card.

Rad-Com Soft-Control

Soft-Control software provides remote access to your radio's functions via a serial link from your PC. Using the radio's built-in command set,



the program lets you control the functions of your transceiver from a simple menu. Soft-Control also includes complete maintenance of the radio's memory channels. Memory data can be added, deleted, or edited and then saved to, or restored from disk.

Available immediately for the Kenwood TS-440S and IBM PC or compatible, other radio-computer combinations are expected to be available soon. The program can be purchased directly from Rad-Com and sells for \$59.95.

For more information, or to order contact: Rad-Com, P.O. Box 1166, Pleasanton, California 94566.

Circle #308 on Reader Service Card.

4-digit sequence decoder and "QUAD" option

The new model TSDQ 4-digit sequence decoder replaces the TSD decoder. Its features include a DPDT 2-A relay, on board 5-volt regulator, digit valid indicator, and expansion connector. Connections to the board are via a 24-pin card-edge connector, which provides quick disconnect and expansion with the new Model "QUAD" 4-relay expansion card.

The TSDQ operates as a stand-alone 2-4 digit touchtone sequence decoder. Output may be either latching or momentary control of the DPDT relay. All 16 digits are output to the card-edge connector and can be used for single digit commands. The relay turns on when it receives a 4-digit code and turns off when the code is received again. When the QUAD option is plugged in, four DPDT relays may be turned on and off with individual access codes. A master "on" code, followed by the relay number, turns on a relay; a master "off" code, followed by the relay number, turns the relay off. These relay on/off codes can be a total of 3-5 digits long. In addition to the relay outputs there are four transistor outputs to provide LED readouts of the relay states, or act as control voltage for other devices. All output connections are via a 24-pin card-edge connector which uses the same pin numbers for all inputs as the TSDQ card. This allows instant compatibility when the QUAD expansion card is added.

Model "TSDQ" is \$79.95 including 24-pin edge connector. Model "QUAD" is \$99.95 (requires "TSDQ"). Add \$3.00 shipping. California residents add 6 percent.

Additional information can be obtained by contacting, Engineering Consulting, 583 Candlewood Street, Brea, California 92621.

NCG Co. introduces new items

NCG Co. has the following new items available:

•**900-MHz mobile antenna.** Model no. CMW3-71 is a 5/8-wave \times 3-step wide-band

antenna. Gain is 7.14 dB, maximum power is 50 watts. Length is 2'7". Frequency for a 1.5 VSWR is 910-940 MHz, the base has a fold-over design for low garage parking.

•**Dual-band UHF/1.2-GHz mobile antenna.** The Model CHL-120 is a wide-band low VSWR mobile antenna for the high frequencies. Gain is 2.15 dB for UHF and 5.6 dB for 1.2 GHz. Maximum power is 50 watts, VSWR is 1.8 or less, length is 1'2". Simulcast operation is possible when used with the CF-413 duplexer.

•**CM-900 Mini Meter.** Designed for the 900-MHz band, insertion loss is less than 0.2 dB; measurable power is from 0 to 120 watts. SWR is 1.0-5, power range 10/120W accuracy is 0.55 \pm , dimensions are 2.25"W \times 2.55"H \times 1.1"D.

•**CM-300 Mini Meter.** Designed for the 200-240 MHz, insertion loss is less than 0.2 dB; measurable power is from 0-60 watts. SWR measurement 1.0-5 to 1. Accuracy is 0.50 \pm , dimensions are 2.25"W \times 2.55"H \times 1.1"D. The CM-300 is equipped with UHF connectors.



•**Low-loss coax mounting kits.** The CK-5LX is the 5DQEV + RG188A/u. The CK-5LX is usable from 1 MHz to 1.5 GHz. The CK-3LX is the 3.5DQEV + RG188A/u. The CK-3LX is usable from 1 MHz to 900 MHz. The loss for the coax is: 3.5DQEV at 400 MHz 3.5, at 1000 MHz 5.6 per 100 feet. 5D-QEV at 400 MHz 3.2, at 1000 MHz 5.3.

For further information on any of these items, contact NCG Co. 1275 N. Grove Street, Anaheim, California 92806.

Circle #309 on Reader Service Card.

(continued on page 125)

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CT-50	5 Hz-600 MHz	LESS THAN 25 mV	1 PPM	8	1Hz, 10Hz	189.95
CT-125	10 Hz-1.25 GHz	< 25mV @ 50 MHz < 15mV @ 500 MHz < 100mV @ 800 MHz	1 PPM	9	0.1 Hz, 1Hz, 10Hz	189.95
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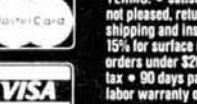
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short circuits Wrong ZIP!

The ZIP code for FAR Circuits (see
W4ULD article, September 1988) was
incorrectly shown as 60188. Please
note that the correct ZIP is 60118. *Ed.*

Correct equations

In equation 4, (see K4IPV column,
August 1988) R3 should have been R1.
Equation 9 should have read:

$$X_{C2} = R2 \sqrt{\frac{R1/R2}{(Q2+1) - (R1/R2)}}$$

Equation 12 should have read:

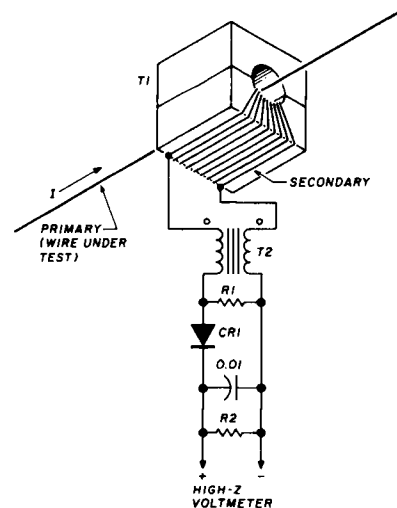
$$X_{CIB} = \sqrt{\frac{R1}{R2(Q2+1)} - 1}$$

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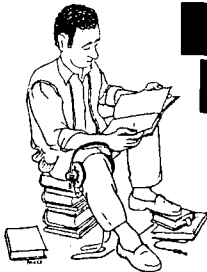
Corrected drawing

Corrected version of fig. 1 for KO1F
ham note "Easy Measurement of An-
tenna Currents," *Ham Radio*, Septem-
ber 1988, page 40.

Ed.



The primary is the antenna feed under test.
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DX FORECASTER

Garth Stonehocker, KØRYW



Winter DX Anomalies

The winter DX season usually has higher signal strengths and lower thunderstorm noise than the summer, particularly on the lower bands. Both of these conditions increase the signal-to-noise ratio at our receivers, making winter the enhanced DX season. These geophysical conditions occur at this time because the sun's subsolar point (spot on earth directly under the sun) moves down to the Southern Hemisphere. The big thunderstorms are located over the southern land masses, so an added F-region hop is needed to propagate to those of us in the northern mid-to-high latitudes. The amount of signal absorbed is related to the solar zenith angle present at the D-region transmit points on the signal's propagation path. The southern position of the sun lowers this angle and, in turn, lowers the absorption.

The anomaly of this ordinarily improved wintertime signal is the five to six day periods of 20 to 40-dB weaker signals (more like summertime) through the mid-to-high latitude paths providing our communication links to European, Asian, and Japanese Amateurs. I've discussed the cause in detail in past December columns; it affects those latitudes in 90 degree increments of longitude. The latitudes directly opposite each other have higher than normal winter signals, and those opposite but on different longitudes have

lower than normal winter signals. The areas rotate 30 degrees (two time zones) per day, while decreasing from 65 down to 30 degrees latitude in the five days of rotation.

To take advantage of the decreased absorption that provides strong DX signals on east, west, and transpolar paths, access WWV or the bulletin board to keep track of the daily geomagnetic A value during the winter (mainly January). Continue to keep track after each A value of 15 or higher, until a STRATWARM is given. Then, consult your map or globe to find the 90-degree position between the location given for the STRATWARM and its 180-degree companion. Coordinate your beam bearings and the DX path control points (1200 miles from the QTHs "on" the great circle) with the areas of lower absorption on both ends, or at least one end. If the area isn't right for your DX on that particular day, you can forecast — at 30 degrees of longitude and lower latitude per day — when you can expect good results during the five to six days to come.

Another geophysical winter effect that seems like an anomaly is the higher wintertime maximum usable frequencies (MUFs). True, the D, E, and lower F region have larger electron densities in summer, but the maximum density of the F-region (which usually sets the day's MUF) peaks during the winter instead. This peak isn't as broad (measured by hours of the day) as it is in the summer — it's narrower and higher. You have to be right there when the band opens (on 10 meters,

for instance) to catch these few hours. This same effect makes the one-long-hop transequatorial propagation possible in the evenings.

Last-minute forecast

The second and third full weeks of the month should have excellent higher frequency (10 to 30 meter) DX band openings. Expect both long-skip and extra DX transequatorial openings from high MUF build-up during the day and evenings. Some short-skip sporadic E openings might even help your DX. The lower bands should be best the first and fourth weeks. (This includes Christmas weekend for those trying out some new equipment from under the tree!) Low bands are a great way to spend these long nights by the fire with friends.

The Geminids meteor shower, which peaks on December 13th and 14th, will provide the richest and most reliable display of the year, with rates of 60 to 70 per hour. Because optical observations may be difficult or impossible to make during periods of poor December weather, determine the actual numbers by radio reception. A smaller version of the shower will occur on December 22nd. The full moon appears on the 23rd, and lunar perigee happens on the 16th. Winter solstice is on December 21st at 1528 UTC.

Band-by-band summary

Ten, 12, 15, and 20 meters will be open from morning until early evening almost every day to most areas of the world. The openings on the higher of these bands will be shorter and occur closer to local noon. Transequatorial propagation on the higher bands will probably occur toward evening, during times of high solar flux and disturbed geomagnetic field conditions.

GMT	WESTERN USA									
	PST	N	NE	E	SE	S	SW	W	NW	
0000	4:00	40	40	20	15	12*	12	10	15	15
0100	5:00	20	40	20	15	12	10	10	20	20
0200	6:00	30	40	20	20	12	10	12	20	20
0300	7:00	30	40	20	20	15	10	15	20	20
0400	8:00	30	40	20	20	15	12	20	30	30
0500	9:00	30	40	20	20	20	12	20	30	30
0600	10:00	40*	40	20	20	20	15*	20	30	30
0700	11:00	30	40	20	20	20	15	20	30	30
0800	12:00	30	40	20	20	20	15	20	30	30
0900	1:00	40	40	20	20	20	15	20	30	30
1000	2:00	40	40	20	20	20	15	20	30	30
1100	3:00	40	40	20	20	20	20	20	40	40
1200	4:00	40	40	15	20	30	20	20	40	40
1300	5:00	40	40	12	15	20	20	20	40	40
1400	6:00	40	20	12	15	20	20	20	40	40
1500	7:00	40	20	10	12	15	20	20	40	40
1600	8:00	30	20	10	12	15	20	20	40	40
1700	9:00	30	20	10	12	15	20	20	40	40
1800	10:00	40	30	10	10	15	15	20	40	40
1900	11:00	40	30	12	10	12	15	15	40	40
2000	12:00	40	30	12	10	12	15	15	20	20
2100	1:00	40	30	15	10	12	12	12	20	20
2200	2:00	40	30	15	10	12	12	12	20	20
2300	3:00	40	30	15	12	12*	12	10	15	15

GMT	MID USA									
	MST	N	NE	E	SE	S	SW	W	NW	
0500	4:00	40	40	20	15	12	10	10	20	20
0600	5:00	30	40	20	15	12	10	12	30	30
0700	6:00	30	40	20	20	15	12	15	30	30
0800	7:00	30	40	20	20	15	12	20	30	30
0900	8:00	30	40	20	20	20	15	20	30	30
1000	9:00	30	40	20	20	20	20	20	30	30
1100	10:00	40	40	20	20	20	20	20	30	30
1200	11:00	40	40	20	20	20	20	20	30	30
1300	12:00	40	40	20	20	20	20	20	40	40
1400	1:00	40	40	20	20	20	20	20	40	40
1500	2:00	40	40	20	20	20	20	20	40	40
1600	3:00	40	40	15	20	20	20	20	40	40
1700	4:00	40	40	12	15	20	20	20	40	40
1800	5:00	40	40	12	15	20	20	20	40	40
1900	6:00	20	20	12	15	20	20	20	40	40
2000	7:00	20	20	12	15	20	20	20	40	40
2100	8:00	30	20	10	12	15	20	20	30	30
2200	9:00	30	20	10	12	15	20	15	40	40
2300	10:00	30	20	10	10	15	15	15	40	40
2400	11:00	30	30	10	10	12	15	20	40	40
2500	12:00	40	30	10	10	12	15	20	40	40
2600	1:00	40	30	12	10	12	15	15	40	40
2700	2:00	40	30	12	10	12	12	12	40	40
2800	3:00	40	30	15	12	12*	12	12	20	20
2900	4:00	40	30	15	12	12*	12	10	20	20
3000	5:00	40	30	15	12	12	12	10	20	20

GMT	EASTERN USA									
	EST	N	NE	E	SE	S	SW	W	NW	
7:00	4:00	40	40	20	15	15	15	15	12	30
8:00	5:00	30	40	20	15	15	15	20	20	30
9:00	6:00	30	40	20	20	20	20	20	30	30
10:00	7:00	30	40	20	20	20	20	20	30	30
11:00	8:00	30	40	20	20	20	20	20	30	30
12:00	9:00	30	40	20	20	20	20	20	30	30
1:00	10:00	40	40	20	20	20	20	20	40	40
2:00	11:00	40	40	20	20	20	20	20	40	40
3:00	12:00	40	40	20	20	20	20	20	40	40
4:00	1:00	40	40	20	20	20	20	20	40	40
5:00	2:00	40	40	20	20	20	20	20	40	40
6:00	3:00	40	40	20	20	20	20	20	40	40
7:00	4:00	40	40	20	20	20	20	20	40	40
8:00	5:00	20	20	12	15	20	20	20	40	40
9:00	6:00	20	20	12	15	20	20	20	40	40
10:00	7:00	30	20	10	12	15	20	15	30	30
11:00	8:00	30	20	10	12	15	20	15	40	40
12:00	9:00	30	20	10	10	15	20	20	40	40
1:00	10:00	30	20	10	10	12	15	20	40	40
2:00	11:00	30	20	10	10	12	15	20	40	40
3:00	12:00	40	30	12	10	12	15	15	40	40
4:00	1:00	40	30	12	10	12	10	12	40	40
5:00	2:00	40	30	15	10	12*	10	12	20	20
6:00	3:00	40	30	15	10	12*	10	10	20	20
7:00	4:00	40	30	15	12	12*	10	10	20	20
8:00	5:00	40	30	15	12	12*	10	10	20	20
9:00	6:00	40	30	15	12	12	10	10	20	20

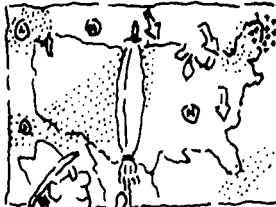
The italicized numbers signify the bands to try during the transition and early morning hours, while the standard type provides MUF during "normal" hours.
 *Look at next higher band for possible openings.

You'll find 30 and 40 meters useful almost 24 hours a day. Daytime conditions will resemble those on 20 meters. Skip distances and signal strengths may decrease during midday on days that coincide with these higher solar flux values. Expect good night-time DX, except after days of high MUF conditions and during geomagnetic disturbances. Look for DX from unusual places on eastern, northern, and western paths during this time. The usable distance is expected to be somewhat less than on 20 in the daytime and greater than on 80 at night.

Eighty and 160 meters will exhibit short-skip propagation during daylight hours and lengthen for DX at dusk. These bands follow the darkness regions opening to the east just before your sunset, swinging more to the south around midnight, and ending up in the Pacific areas an hour or so before dawn.

Article K

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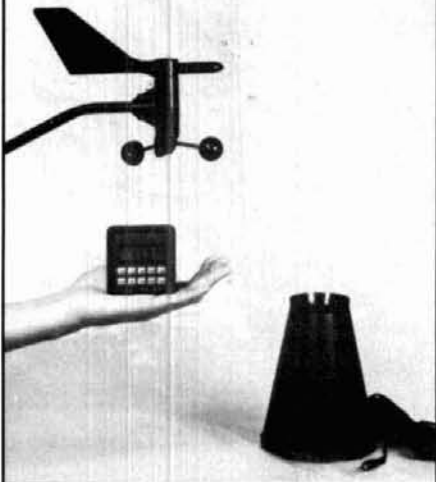


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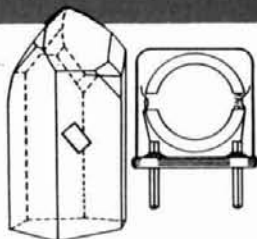
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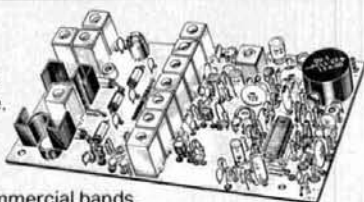
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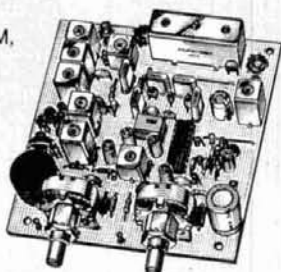


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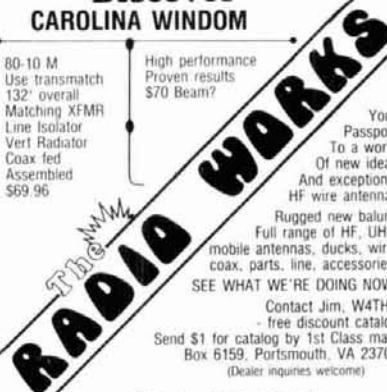
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ELMER'S NOTEBOOK

Tom McMullen, W1SL

SSB basics — receiving the signal

This is the second half of a discussion of SSB begun in November. Last month I explained how SSB was generated and translated (heterodyned) to the Amateur bands, and touched on some benefits of using that mode of communication. This month, I'll look at how SSB is received and talk about the peculiarities of the mode that make receiver design a bit tricky.

The first part of a receiver that SSB signals encounter after being picked up by the antenna is the front end, or RF amplifier stage(s). There are no unusual features making the front end for SSB any different from that for any other mode. The usual criteria apply — low noise, freedom from overload by strong signals, and enough selectivity to reject out-of-band signals.

The next stage encountered is an i-f amplifier. Some receivers have two intermediate frequencies with an extra conversion to get from one to the other; others have only one conversion to a single i-f. Common frequencies are 10.7, 9.0, and 5.5 MHz, but others can work as well. In either case, a local oscillator is mixed with the incoming SSB signal to produce the i-f. This is done in a heterodyning system, just as it was at the transmitting end to get the generated sidebands on the ham band of interest. In the example given

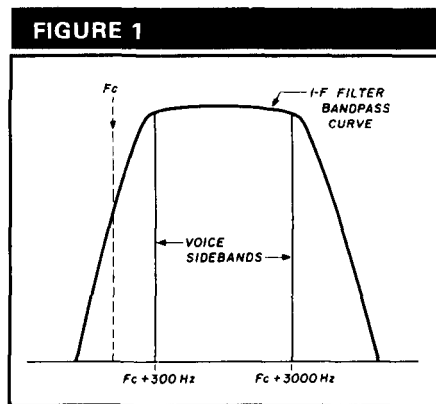


FIGURE 1
A single-sideband signal as it appears in the receiver i-f stages is a band of audio frequencies covering approximately 300 to 3000 Hz. This signal should be practically identical to the one generated by the balanced modulator and filter combination discussed in last month's column.

last month, a 19.5-MHz signal was mixed with 9.0-MHz SSB to produce output on 28.5 MHz. The same process works in reverse — mixing 28.5-MHz SSB with a local oscillator of 19.5 MHz produces an i-f at 9.0 MHz. These 9-MHz sidebands are pretty much carbon copies of the ones generated by the balanced modulator and then filtered before being amplified and transmitted. In fact, many of today's popular transceivers use the very same filters for the i-f in receiving a signal as they do for generating the sidebands in a transmitter. The filter is switched between the receiving and transmitting circuitry by means

of diodes and/or transistors, and thus made to serve double duty. The resulting output from this filter is a range of voice "sidebands" that covers approximately 300 to 3000 Hz, just as in the transmitter. (See fig. 1.)

Putting the carrier back

At this point, a common diode detector like that used for AM signals wouldn't be able to translate these sidebands into anything useful. The next step is to add an RF carrier in exactly the same relationship as the one that was suppressed in the transmitter. This isn't hard to do. All it takes is an oscillator at the right frequency and a mixer to combine the sidebands with the signal from that oscillator. You'll then have an AM carrier with one sideband, which an ordinary diode detector can turn into audio. Some early attempts at receiving SSB with the AM/CW receivers of the day showed how poor an idea this is.

In the early days of SSB, the receiver's beat-frequency oscillator (BFO) used for CW reception was pressed into service to supply the missing carrier, and the AM detector took over from there. The trick was to tune in the sidebands for maximum loudness (even if you couldn't understand the voice), then move the BFO around until you heard something you could understand. Hopefully, you could get a somewhat normal-sounding voice



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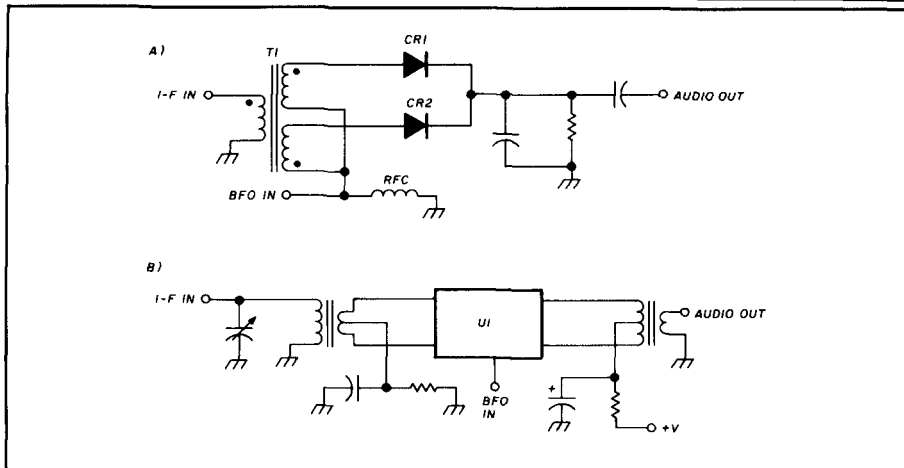
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FIGURE 2



Simplified versions of two product detector circuits. Diodes, as at A, involve the least number of components and offer great simplicity. The dots on T1 indicate wiring polarity. An integrated circuit at B can provide gain and increased sensitivity. Bias and decoupling components for U1 are not shown.

out of this. The poor quality, frequency drift, and constant "tweaking" to keep the signal tuned in, turned many hams away from this "new mode".

Better circuits were not long in coming, and their improvements led to today's increased efficiency and better quality SSB. One of these circuits is called the "product detector." This type of circuit produces an output only when both inputs are present; that is, the BFO must be on and the SSB signal must be present before the detector provides an audio signal output. Diagrams of two types of product detector are shown in fig. 2.

There are many versions of product detectors and most work quite well. Some equipment manufacturers are going for the simplicity of the diode circuit; others are using integrated circuit types, often combining the detector function with an audio preamplifier or some other part of the receiver circuit. Another type of detector circuit uses JFETS or MOSFETS as the active element.

Sounds good but...

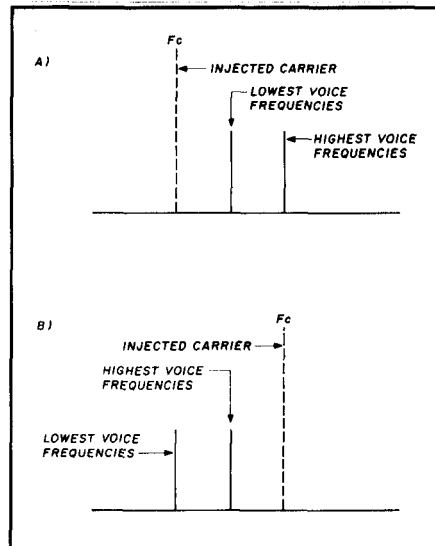
Sometimes you get funny "audio" when you tune in an SSB signal. To understand how this happens, let's look at fig. 3. In 3A, the carrier is

placed in its correct relationship to the sidebands. In this example, the signal is upper sideband so the carrier is below, and the lower voice frequencies are closest to the carrier. The higher frequencies are farther from the carrier, just as they were when the original sidebands were generated.

Switch the carrier to the other side of the sidebands, as in fig. 3B and watch what happens. The higher voice frequencies are now close to the carrier, while the low frequencies are farther away. The result is an "inverted" voice that's impossible to understand. The range of speech frequencies has been inverted.

This "inversion" is something that receiver designers have to watch for when they heterodyne signals from the various Amateur bands down to an i-f, or mix generated SSB with a local oscillator to get to an Amateur band. For instance, look at my earlier example of mixing 28.5 MHz with 19.5 MHz to obtain 9-MHz i-f output. You can also get a 9-MHz difference (i-f) by mixing 28.5 MHz with 37.5 MHz, but the signal will be inverted compared to that obtained with 19.5 MHz. The 9.0-MHz sidebands in your detector will sound just as scrambled as if you tuned them in wrong, or selected the wrong position of your upper/lower

FIGURE 3



Placing the local carrier on the wrong side of the SSB signal can produce unintelligible audio. At A, the carrier is correctly placed below the upper sideband signal and the audio is "right-side-up." If the carrier is placed on the other side, as at B, the audio is inverted; i.e., the higher voice frequencies are near the carrier and the lower ones are farther from it. The resulting inverted voice frequencies are unreadable.

sideband switch. You can correct this inversion by selecting the other sideband to "uninvert" the audio. In some receivers and transceivers, just such a scheme is used in order to use simplified circuitry for local oscillators. A 9.0-MHz SSB signal mixed with 5.0 MHz produces 4.0 MHz for 75-meter work ($9.0 - 5.0 = 4.0$), and can also produce 14.0 MHz for 20 meters ($9.0 + 5.0 = 14.0$). The sidebands will be inverted for one band, so the correct BFO crystal for generating (or receiving) the signal must be used as required to produce audio that is "right-side-up." Some early receivers had colored dial and knob markings as a reminder to switch to upper or lower sideband to match the Amateur band you were listening to. Incidentally, in the frequency-mixing example just used, the sidebands are not the only inversion — look what happens if you make the 5.0-MHz oscillator signal variable (VFO) to tune across the band. In the 75-meter case, if you increase the VFO frequency to 5.1 MHz, subtracting that

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from 9.0 shows that you are now tuned to 3.9 MHz. So to tune "down" the band, you *increase* the frequency of the VFO. For 20 meters, the opposite is true — $5.1 + 9.0 = 14.1$ MHz. This is a case where you must keep your pluses and minuses straight!

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An additional benefit of modern improved circuitry for receiving SSB is better reception of CW. The product detector, with its lower noise, helps in weak signal reception. The improved oscillator stability needed for constant voice quality also helps the CW signal stay put on the dial. The SSB filters used in the receiver i-f work okay for CW reception, but most people who use code a lot prefer an additional set of filters that narrow the "window" to only that necessary to receive a few hundred hertz of spectrum. Why listen to more signals than you absolutely have to?

The product detector also works for AM reception; just turn off the local BFO and let the original carrier ride through. The narrow filter for SSB will restrict AM quality somewhat, but it's still adequate. Wider filters are available that can be switched into the i-f system for AM use if better audio quality is desired.

I'd like to thank those of you who have taken the time to write to me about what you've seen in this column, and on many other interesting subjects. I can't answer each letter personally, but each is carefully read. Your thoughts and comments are appreciated. The article about "Q" signals generated several interesting letters (as did the mention of "Z" signals in that article). Some letters provided me with new information. Again, many thanks to each of you.

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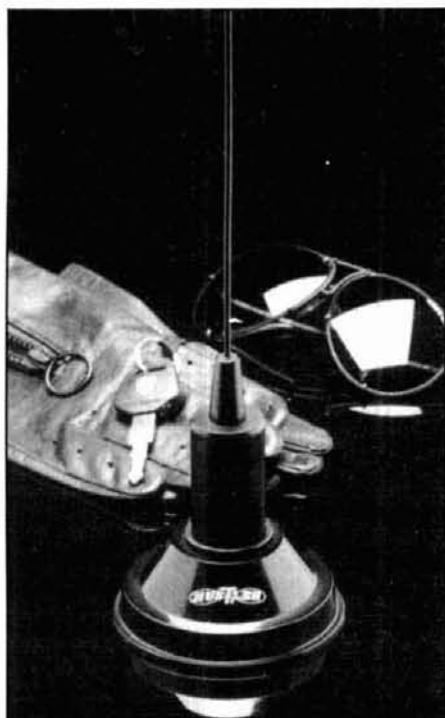
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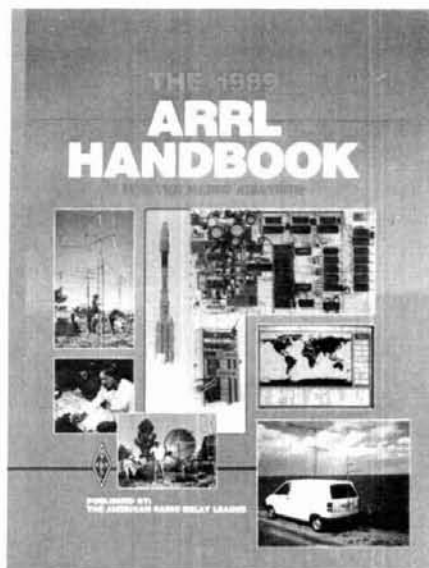
The 1200-page sixty-sixth edition contains over 2100 tables, figures and charts. The new Handbook is better than ever with revised information on phase noise measurement, direct frequency synthesis and spread spectrum communication techniques. The section on repeaters has been updated including a new CW identifier circuit. You'll find new spectrum analyzer and oscilloscope material, as well as several new projects in the test equipment chapter.

As always, we've added a host of new construction projects to this new edition. Just some of the new projects include: A 500-MHz frequency counter, 160 through 10 meter legal limit amplifier, simple CMOS keyer project, digital audio memory keyer and a L/Q meter for measuring coil inductance.

But that's not all. You'll find many other popular construction projects that can be built in a weekend such as power supplies and VHF/UHF preamps. For the more ambitious builder there are projects like the 1.8 MHz QSK transverter (there are VHF/UHF transverter projects too) and there are many amplifier designs to suit your needs from HF through microwaves.

The Handbook has always been famous as a reference for component data and you will find an entire chapter devoted to everything from transmitting tube and transistor specifications to aluminum tubing sizes. Satellite enthusiasts will find that the digital TR sequencer will add operating convenience to your station. Of course, you'll find the most up-to-date information on digital techniques, and the video communications chapter is packed with information not only on SSTV, ATV and FAX but Weather FAX as well. QRP enthusiasts will find the famous "Cubic incher" transmitter; not much bigger are the QRP SWR indicator and QRP Transmatch. There is also a VXO-controlled 6-watt CW transmitter for your favorite band between 80 and 15 meters. There are a number of useful station accessories that you can build like DTMF encoders and decoders, PIN-diode TR switch, digital PEP wattmeter and SWR calculator, Transmatches and dummy loads.

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Here is a description of what is covered in the Handbook:

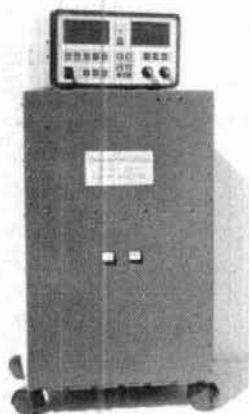
The first 5 chapters serve as an introduction and cover: basics of Amateur Radio, electrical fundamentals, radio design technique and language, and solid state fundamentals. Vacuum tube principles as they pertain primarily to high power amplifier design are also presented in these introductory chapters. There are 12 chapters devoted primarily to these radio principles: power supplies, audio and video, digital basics, modulation and demodulation RF transmitters, receivers, transceivers, repeaters, power amplifiers, transmission lines and antenna fundamentals. Another 4 chapters cover voice, digital, image and special modulation techniques. The RF spectrum, propagation and space communications are covered in 2 chapters. The construction and maintenance section has 12 chapters of useful projects ranging from power supplies and antennas through digital equipment. You'll find up-to-date component data that the Handbook is famous for. The final 5 chapters cover how to obtain your license, station design and operation, interference, monitoring and direction finding. An abbreviations list, huge index and etching patterns make up the balance of the book.

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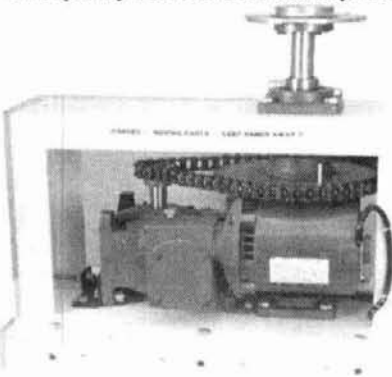
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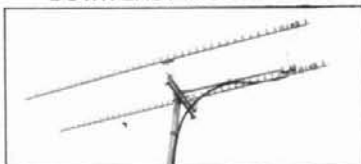
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(continued from page 104)

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The 80i-kW is available for immediate delivery at a U.S. list price of \$395 from over 600 distributor locations in the United States, or through Fluke's worldwide sales network.



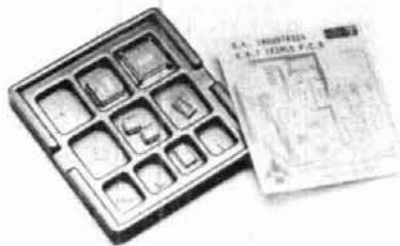
For more information on the Fluke 80i-kW Current/Power Probe, in North America and non-European countries write to John Fluke Mfg. Co., Inc., P.O. Box C9090, Everett, Washington 98206 or call toll free 800-443-5853, ext. 77. In Europe, contact Philips Test and Measurement, Building HFK, 5600 MD Eindhoven, The Netherlands.

Circle #311 on Reader Service Card.

New SMT trials kit

OK Industries has introduced the SMT-K1, a kit that enables those who work with surface mounted devices to evaluate, practice, or train on assembly, production, or rework techniques.

The kit includes a full range of surface-mounted components including chip capacitors, transistors, PLCCs, and 100-pin gull-wing flat packs. The SMT-K1 also contains a trial board designed to accommodate a wide variety of components. The board and components come complete in a reusable conductive tray.



The list price for the SMT-K1 is \$64.95.

For further information contact OK Industries, 4 Executive Plaza, Yonkers, New York 10701.

Circle #312 on Reader Service Card.

New series of Kelvin Probes

O.K. Industries Inc. Electronics Division introduces a new series of Kelvin Probes. The TK800 Series probes are very low resistance, precision test lead kits ideal for LCR bridges or microhm meters.

Circuit connection: (2) flat tweezers with special gripping surfaces ensure precise contact to the components to be measured. Contacts are gold plated for optimum electrical performance. An additional alligator clip, ground lead connection is also provided.

Instrument connection: (4) BNC or banana connectors with color-coded strain-relief boots. Specifications: 250V rms, 5A current with 0.8M cable length.

The TK800 series is Ex-stock. The list price is \$119.00.

For details contact OK Industries, 4 Executive Plaza, Yonkers, New York 10701, 1-800-523-0667.

Circle #312 on Reader Service Card.

Multi-mode autopatch and repeater controller

Connect System Inc.'s new Private Patch V can be user programmed into four selectable operating modes: Sampling Patch (vox enhanced), Vox Patch (can operate through remotely located repeaters), Duplex Patch, and Repeater Controller with Duplex Patch (perfect for club systems).



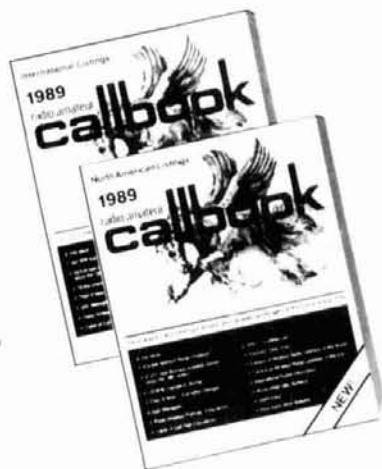
Private Patch V has a built-in keyboard and digital display that gives you complete control of all features and operating modes. Features include: a ninety number auto-dialer, last number redial, remote hook-flash, keyboard programmable CW ID, toll protection, 1-5 digit access code, 2-5 digit secret toll override code, telephone remote base, remote controlled relay, and regenerated tone/pulse dialing.

A plug-in CTCSS board that converts all modes to CTCSS operation (32 selectable tones) and an Electronic Voice Delay board which enhances performance in vox mode are optional.

For more information, contact: Connect Systems Inc. 23731 Madison Street, Torrance, California 90505.

Circle #313 on Reader Service Card.

1989 CALLBOOKS



THE QSL BOOK!

Continuing a 68 year tradition, we bring you three new Callbooks for 1989, bigger and better than ever!

The North American Callbook lists the calls, names, and address information for 495,000 licensed radio amateurs in all countries of North America, from Canada to Panama including Greenland, Bermuda, and the Caribbean islands plus Hawaii and the U.S. possessions.

The International Callbook lists 500,000 licensed radio amateurs in countries outside North America. Its coverage includes South America, Europe, Africa, Asia, and the Pacific area (exclusive of Hawaii and the U.S. possessions).

The 1989 Callbook Supplement is a new idea in Callbook updates, listing the activity in both the North American and International Callbooks. Published June 1, 1989, this combined Supplement will include thousands of new licenses, address changes, and call sign changes for the preceding 6 months.

Every active amateur needs the Callbook! The 1989 Callbooks will be published December 1, 1988. Order early to avoid disappointment (last year's Callbooks sold out). See your dealer now or order directly from the publisher.

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Name _____ Call _____

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READER SERVICE #	PAGE #	READER SERVICE #	PAGE #
130 - Ace Communications, IN	36	* KB1T	116
163 - Advanced Receiver Research	92	159 - KComm, The Ham Store	87
150 - AEA	74	* Kenwood USA Corporation	2, 5, 7, CIV
170 - Aerospace	94	115 - Larsen Antennas	15
202 - AG6K	124	169 - N.E. Litsche	94
134 - All Electronics Corp	44	196 - Madison Electronics Supply	121
175 - Alpha Delta Communications	98	180 - Magnaphase Industries, Inc	113
189 - AMC Sales, Inc	116	127 - Glen Martin Engineering, Inc	36
142 - Ameritron	66	171 - The Meadowlake Corp	94
185 - AMSAT	114	113 - MFJ Enterprises	8
122 - Antennas West	21, 116, 120	136 - Michigan Radio	50
120 - Antique Radio Classified	18	146 - Micro Control Specialties	72
195 - ARRL	122	204 - Missouri Radio Center	127
167 - Ashton ITC	94	121 - Mobile Mark, Inc	21
* Associated Radio	116	143 - Monitoring Times	
132 - Astron Corp	40		
193 - ATFab Computers and Electronics	120	179 - Motron Electronics	113
* Barker & Williamson	10	154 - NCG	85
* Barry Electronics	103	* Nema Electronics	91
186 - Bilal Company	114	181 - Nuts & Volts	112
123 - Bird Electronics	25	126 - Wm. M. Nye Co. Inc	34
173 - Buckmaster Publishing	97	206 - OPTOelectronics	128
187 - Buckmaster Publishing	114	114 - P.C. Electronics	10
188 - Buckmaster Publishing	116	151 - P.C. Electronics	77
* Buckmaster Publishing	50	137 - Pac-Comm Packet Radio Systems, Inc	50
200 - Burghardt Amateur Center	124	128 - Pipo Communications	36
* Butternut Electronics	25	205 - Radio Amateur Callbook	126
125 - C&S Sales	28	190 - The Radio Works	116
* Caddell Coil Corp	94	131 - Radio Shack	39
129 - CIE	36	177 - Ramsey Electronics, Inc	105
156 - Communication Concepts, Inc	84	148 - The RF Connection	72
139 - Communications Specialists	57	145 - RF Enterprises	73
191 - Computeradio	116	160 - Software Systems	87, 98
112 - Connect Systems Inc	1	157 - Stridsburg Engineering Co	84
184 - Crystek Crystals	114	161 - STV/OnSat	90
* Cushcraft Corp	17	182 - Synthetic Textiles, Inc	98
144 - Cushcraft Corp	71	178 - Tel-Com	113
194 - Cygnus-Quasar Books	120	192 - Thermax	120
117 - Datacom, International	17	* Tropical Hamboree	30
168 - Dick Smith Electronics	94	* Universal Radio	62
118 - Doug Hall Electronics	18	155 - Van Gorden Engineering	84
201 - Down East Microwave	124	162 - Vanguard Labs	91
140 - EGE, Inc	56	116 - Varian EIMAC	16
198 - Electronic Equipment Bank	123	164 - VHF Communications	92
199 - Electronic Equipment Bank	123	165 - W9INN Antennas	92
* Engineering Consulting	58	174 - Western Electronics	97
* Fox Tango Corp	113	147 - Wi-Comm Electronics Inc	72
203 - Gallatin Radio Supply	124	207 - Yaesu USA	CIII
* Gary Appel	92	158 - E.H. Yost Co	84
166 - Giffler Shortwave	92		
119 - GTI Electronics	18		
124 - GTI Electronics	25		
152 - Hal-Tronix	77		
141 - Ham Radio Outlet	64, 65		
* Ham Radio's Bookstore	69, 91, 98, 108, 109, 112		
* The Ham Station	30		
* Hamtronics, NY	115		
* Hamtronics, PA	84		
153 - Harris	79		
* Heath Company	63		
133 - Henry Radio	43		
197 - Hustler	121		
111 - ICOM America, Inc	CII		
138 - ICOM America, Inc	55		
* International Crystal Mfg Co, Inc	21		
149 - International Radio	72		
172 - Jun's Electronics	97		
135 - Kantronics	49		

PRODUCT REVIEW/NEW PRODUCT

310 - AVCOM	125
306 - Communications Specialists	70
313 - Connect Systems Inc	125
* Cushcraft Corp	59
301 - DRSI	59
303 - EEB	70
* Engineering Consulting	104
311 - John Fluke Mfg Co Inc	125
304 - ICOM America, Inc	70
302 - Kantronics	70
309 - NCG	104
* Nema Electronics	70
312 - OK Industries	125
308 - Rad-Com	104
305 - Radio Shack	70
307 - RF Prototype Systems	104

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- Its Got It All!

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2-117	10 in/170 out		
3-22	2 in/20 out		
2-211	2 in/110 out		
3-312	30 in/120 out		

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TM-721A DELUXE FM DUAL BANDER

- 2 Meters (138.000-173.995 MHz) 70 cm (438.000-449.995 MHz)
- Receiver Range
- 45 Watts on 2 Meters
- 35 Watts on 70 cm
- 30 Memory Channels

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THE "ANSWERING MACHINE" MOBILE

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- Digital Voice Recorder
- FT-712 RH for 70cm

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MICRO HT'S FOR 2M, 440

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- LCD Readout
- Wideband Coverage
- Up to 3 Watts Output
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FREQUENCY COUNTERS TO 2.4 GHZ

POCKET SIZE
SIZE: 4" H x 3.5" W x 1" D
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8 LED DIGITS • 2 GATE TIMES
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INTERNAL NI-CAD BATTERIES INCLUDED
AC ADAPTER/CHARGER INCLUDED

EXCELLENT SENSITIVITY & ACCURACY

AC-DC • PORTABLE OPERATION

Small enough to fit into a shirt pocket, our new 1.3 GHz and 2.4 GHz, 8 digit frequency counters are not toys! They can actually out perform units many times their size and price! Included are rechargeable Ni-Cad batteries installed inside the unit for hours of portable, cordless operation. The batteries are easily recharged using the AC adapter/charger supplied with the unit.

The excellent sensitivity of the 1300H/A makes it ideal for use with the telescoping RF pick-up antenna; accurately and easily measure transmit frequencies from handheld, fixed, or mobile radios such as: Police, firefighters, Ham, taxi, car telephone, aircraft, marine, etc. May be used for counter surveillance, locating hidden "bug" transmitters. Use with grid dip oscillator when designing and tuning antennas. May be used with a probe for measuring clock frequencies in computers, various digital circuitry or oscillators. Can be built into transmitters, signal generators and other devices to accurately monitor frequency.

The size, price and performance of these new instruments make them indispensable for technicians, engineers, schools, Hams, CBers, electronic hobbyists, short wave listeners, law enforcement personnel and many others.

STOCK NO:

- #1300H/A Model 1300H/A 1-1300 MHz counter with preamp, sensitivity, < 1mV, 27MHz to 450MHz includes Ni-Cad batteries and AC adapter \$169.95
- #2400H Model 2400H 10-2400 MHz microwave counter includes Ni-Cad batteries and AC adapter \$299.95
- #CCA Model CCA counter/counter, for debugging, ultra sensitive, < 50 micro volts at 150MHz! 1-600 MHz with adjustable threshold, RF indicator LED. Includes Ni-Cad batteries and AC adapter \$299.95

ACCESSORIES:

- #TA-100S Telescoping RF pick-up antenna with BNC connector \$12.00
- #P-100 Probe, direct connection 50 ohm, BNC connector \$20.00
- #CC-12 Carrying case, gray vinyl with zipper opening. Will hold a counter and #TA-1000S antenna. \$10.00

✓ 206

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You'll be hard-pressed to beat the performance of Yaesu's new FT-411 handheld.

Let Yaesu's "next generation" handheld lighten your load!

Picking up where our popular FT-209R Series left off, the 2-meter FT-411 will amaze with its astounding array of features!

The brains of a base station. "Sophisticated operation" takes on new meaning in the FT-411. You get 49 memories, plus dual VFOs for quick band-hopping. Keyboard frequency entry. Automatic repeater shift. DTMF autodialer with ten memories of up to 15 digits each. *Built-in CTCSS encode/decode.* Selectable channel steps: 5/10/12.5/20/25 kHz. Programmable band scan with upper/lower limits. Selectable memory scan. And extended receive coverage of 140-174 MHz (MARS/CAP permit required for transmit on 140-150 MHz).

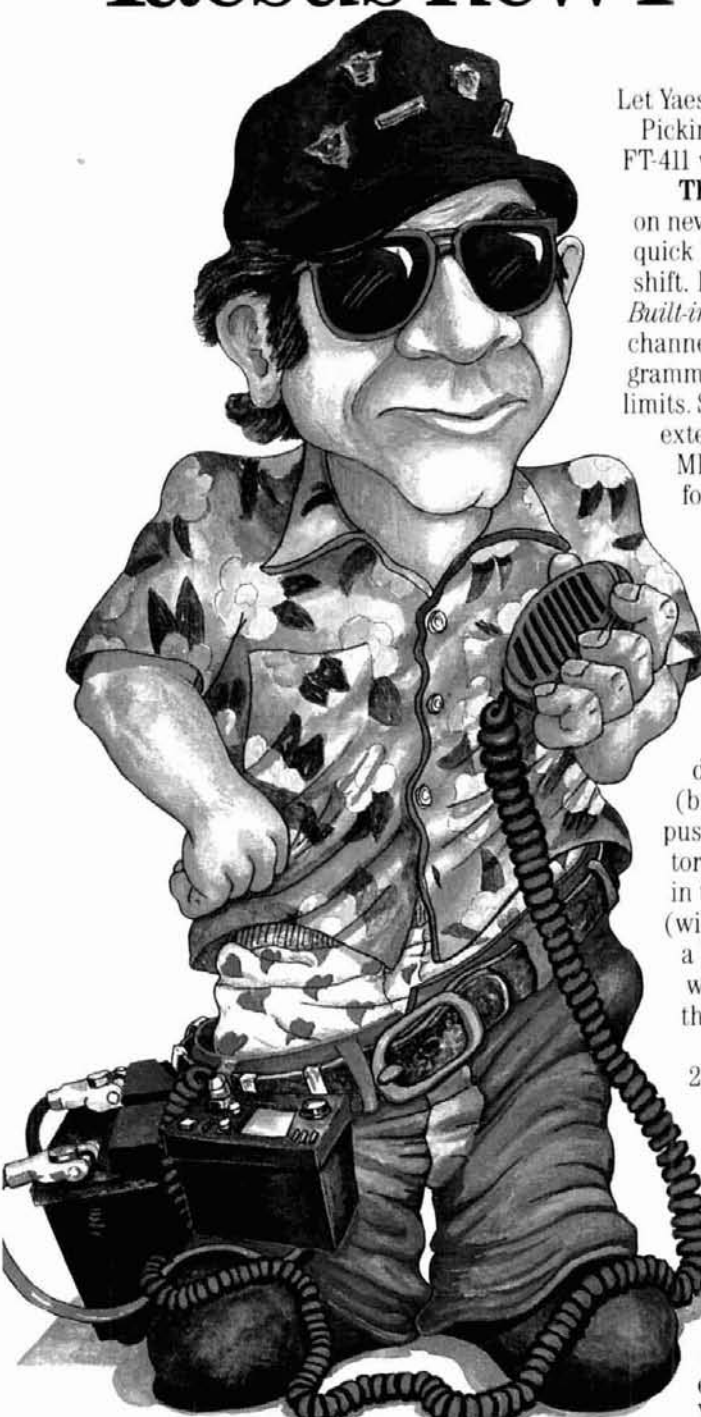
Not bad for a handheld measuring just 55(w) x 32(d) x 139(h) mm (the same size as our FT-23R Series HTs)!

Friendly operation. For operating convenience, the FT-411's keypad features a "do-re-mi" audible command verification. Both the display and keypad can be backlit (brightly!) for night operation at the push of a button. A rotary channel selector allows fast manual tuning. Or key in the frequency directly. Operate VOX (with YH-2 headset option). Plus you get a battery saver to conserve power while monitoring. And a (defeatable) automatic power-off feature that shuts down your radio if you forget to turn it off!

High power capability. The FT-411 comes equipped with the 2.5-watt, 600-mAh FNB-10 battery pack. Try our optional FNB-12 5-watt, 500mAh pack or tiny FNB-9 2.5-watt, 200-mAh pack. Or get 6 watts output by applying 13.8-volts DC from an external power supply.

Swap options with Yaesu's FT-23R Series. Our rugged best-seller's chargers, batteries, and microphones are fully compatible with the FT-411. The FT-23R is the perfect companion for the FT-411, and at a great price!

Try out an FT-411 today. Ask for it now at your local Yaesu dealer. Or call 1-800-999-2070 for a free brochure. And experience the legendary Yaesu HT performance!



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“DX-citing!”

TS-440S Compact high performance HF transceiver with general coverage receiver

Kenwood's advanced digital know-how brings Amateurs world-wide "big-rig" performance in a compact package. We call it "Digital DX-citement"—that special feeling you get every time you turn the power on!

- **Covers All Amateur bands**
General coverage receiver tunes from 100 kHz—30 MHz. Easily modified for HF MARS operation.
- **Direct keyboard entry of frequency**
- **All modes built-in**
USB, LSB, CW, AM, FM, and AFSK. Mode selection is verified in Morse Code.
- **Built-in automatic antenna tuner (optional)**
Covers 80-10 meters.
- **VS-1 voice synthesizer (optional)**



- **Superior receiver dynamic range**
Kenwood DynaMix™ high sensitivity direct mixing system ensures true 102 dB receiver dynamic range. (500 Hz bandwidth on 20 m)
- **100% duty cycle transmitter**
Super efficient cooling permits continuous key-down for periods exceeding one hour. RF input power is rated at 200 W PEP on SSB, 200 W DC on CW, AFSK, FM, and 110 W DC AM. (The PS-50 power supply is needed for continuous duty.)



- **Adjustable dial torque**
- **100 memory channels**
Frequency and mode may be stored in 10 groups of 10 channels each. Split frequencies may be stored in 10 channels for repeater operation.
- **TU-8 CTCSS unit (optional)**
- **Superb interference reduction**
IF shift, tuneable notch filter, noise blanker, all-mode squelch, RF attenuator, RIT/XIT, and optional filters fight QRM.
- **MC-43S UP/DOWN mic. included**
- **Computer interface port**
- **5 IF filter functions**
- **Dual SSB IF filtering**
A built-in SSB filter is standard. When an optional SSB filter (YK-88S or YK-88SN) is installed, **dual** filtering is provided.
- **VOX, full or semi break-in CW**
- **AMTOR compatible**



Optional accessories:

- AT-440 internal auto. antenna tuner (80 m—10 m)
- AT-250 external auto. tuner (160 m—10 m)
- AT-130 compact mobile antenna tuner (160 m—10 m)
- IF-232C/IC-10 level translator and modem IC kit
- PS-50 heavy duty power supply
- PS-430/PS-30 DC power supply
- SP-430 external speaker
- MB-430 mobile mounting bracket
- YK-88C/88CN 500 Hz/270 Hz CW filters
- YK-88S/88SN 2.4 kHz/1.8 kHz SSB filters
- MC-60A/B0/B5 desk microphones
- MC-55 (BP) mobile microphone
- HS-5/6/7 headphones
- SP-40/50B mobile speakers
- MA-5/VP-1 HF 5 band mobile helical antenna and bumper mount
- TL-922A 2 kw PEP linear amplifier
- SM-220 station monitor
- VS-1 voice synthesizer
- SW-100A/200A/2000 SWR/power meters
- TU-8 CTCSS tone unit
- PG-2S extra DC cable.

Kenwood takes you from HF to OSCAR!



Complete service manuals are available for all Kenwood transceivers and most accessories. Specifications and prices are subject to change without notice or obligation.

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