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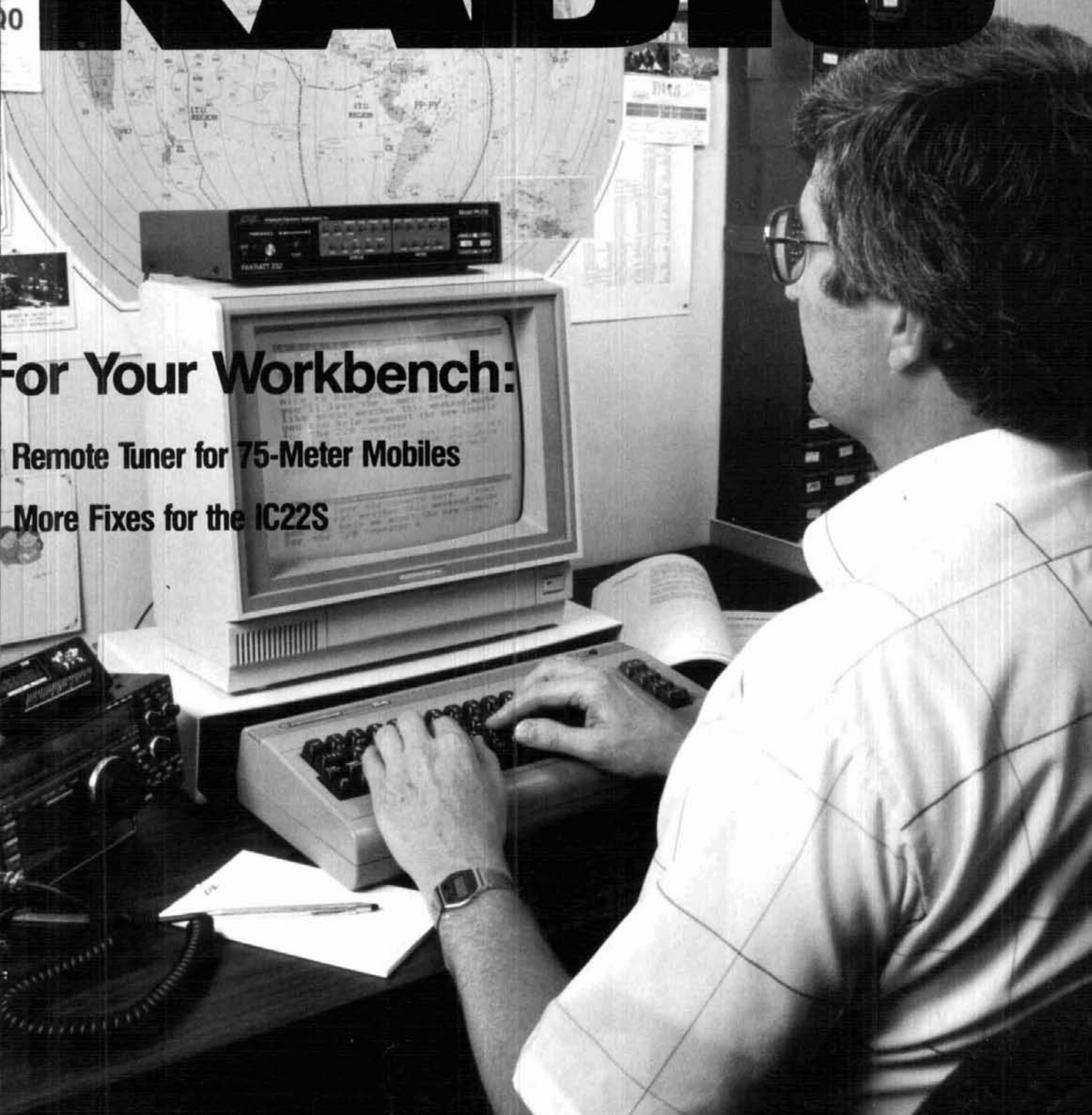
HAM RADIO

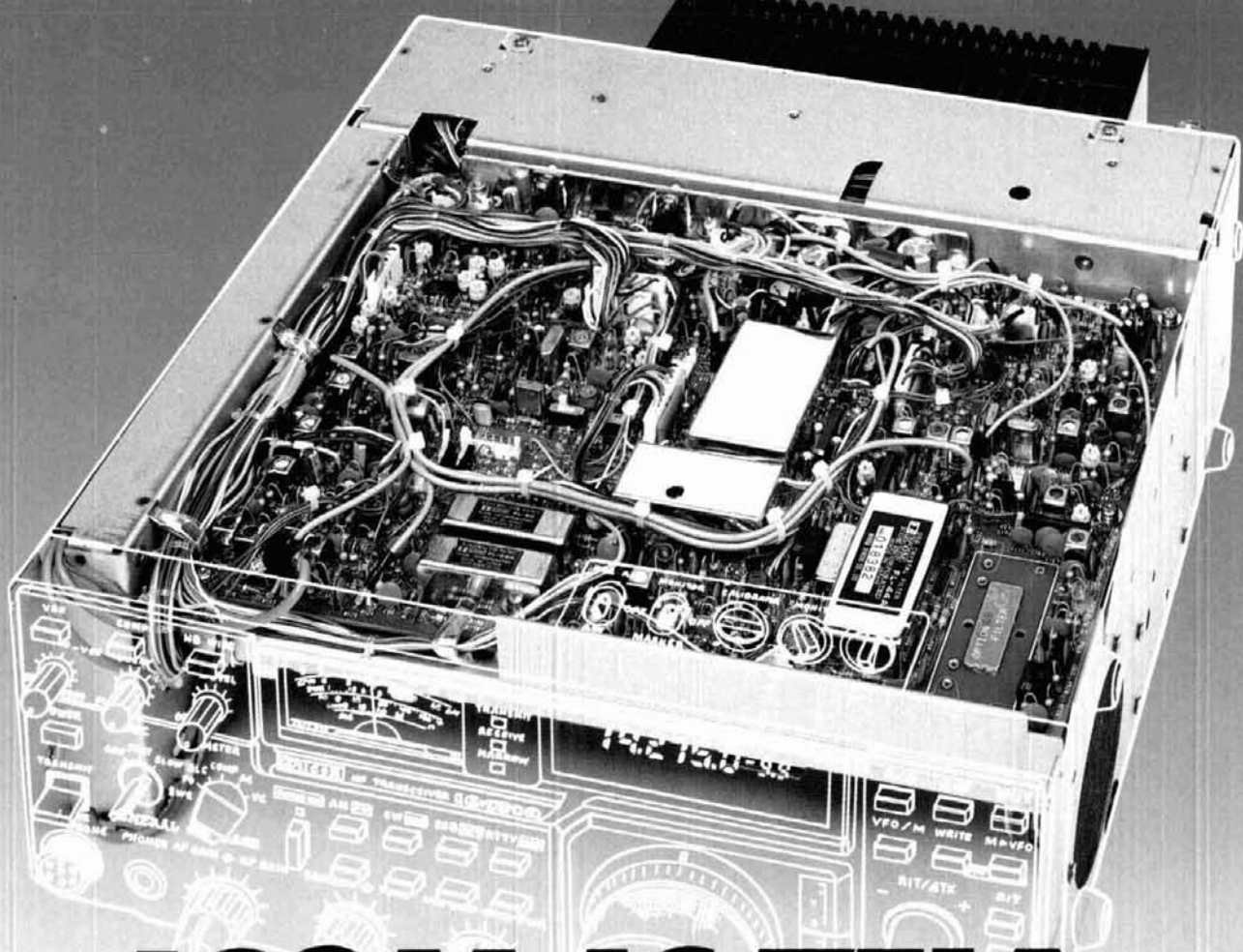
Exploring
Packet Radio
with KISS

For Your Workbench:

Remote Tuner for 75-Meter Mobiles

More Fixes for the IC22S





ICOM IC-751A

"IT'S WHAT'S INSIDE THAT COUNTS!"

- All HF Band Transceiver / General Coverage Receiver
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- All Modes Built-in USB, LSB, FM, AM, CW, RTTY
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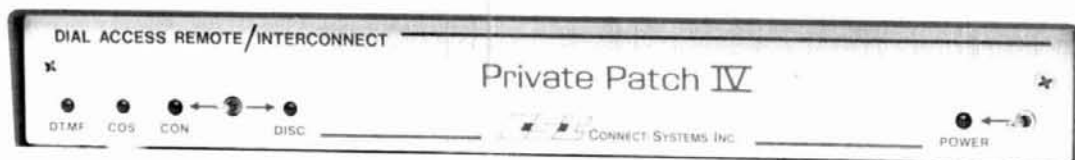
All stated specifications are approximate and subject to change without notice or obligation. All ICOM radios significantly exceed FCC regulations limiting spurious emissions. 751A187

THE ALL NEW PRIVATE PATCH IV BY CSI HAS MORE COMMUNICATIONS POWER THAN EVER BEFORE

- Initiate phone calls from your HT or mobile
- Receive incoming phone calls

NEW! • Telephone initiated control . . .

- ✓ Operate your base station with complete control from any telephone
- ✓ Change frequencies from the controlling telephone
- ✓ Selectively call mobiles using regenerated DTMF from any telephone
- ✓ Eavesdrop the channel from any telephone
- ✓ Use as a wire remote using ordinary dial up lines and a speaker phone as a control head.



The new telephone initiated control capabilities are awesome. Imagine having full use and full control of your base station radio operating straight simplex or through any repeater from any telephone! From your desk at the office, from a pay phone, from a hotel room, etc. You can even change the operating channel from the touchpad!

Our digital VOX processor flips your conversation back and forth fully automatically. There are no buttons to press as in phone remote devices. And you are in full control 100% of the time!

The new digital dialtone detector will automatically disconnect Private Patch IV if you forget to send # (to remotely disconnect) before hanging up. This powerful feature will prevent embarrassing lock-ups.

The importance of telephone initiated control for emergency or disaster communications cannot be overstated. Private Patch IV gives you full use of the radio system from any telephone. And of course you have full use of the telephone system from any mobile or HT!

To get the complete story on the powerful new Private Patch IV contact your dealer or CSI to receive your free four page brochure.

Private Patch IV will be your most important investment in communications.

✓ = NEW FEATURE

- ✓ */# or multi-digit connect/disconnect
- ✓ Fully regenerated tone dialing
 - Pulse dialing
 - Toll protection
 - Secret toll override code
 - Busy signal disconnect
- ✓ Dialtone disconnect
 - CW identification
 - Activity timer
 - Timeout timer
- ✓ Telephone initiated control
- ✓ Regenerated DTMF selective calling
 - Ringout
- ✓ Ringout or Auto Answer on 1-8 rings
 - Busy channel ringout inhibit
- ✓ Status messages
- ✓ Internally squelched audio
 - MOV lightning protection
- ✓ Front panel status led's
- ✓ Separate CW ID level control
- ✓ 24 dip switches make all features user programmable/selectable.

- Connects to MIC and ext. speaker jack on any radio. Or connect internally if desired.
- Can be connected to any HT. (Even those with a two wire interface.)
- Can be operated simplex, through a repeater from a base station or connected directly to a repeater for semi-duplex operation.
- 20 minutes typical connect time
- Made in U.S.A.

OPTIONS

1. 1/2 second electronic voice delay
2. FCC registered coupler
3. CW ID chip



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KENWOOD

...pacesetter in Amateur Radio

THE FIRST
144/220 MHz
Dual Bander!

Double Take!



ACTUAL SIZE FRONT PANEL

TM-621A/721A 144/220 and 144/450 MHz FM Dual Banders

Once again, Kenwood brings you another Dual Bander First! The TM-621A is the first 144/220 MHz FM Dual Bander. The Kenwood TM-621A and TM-721A (144/450 MHz) re-defines the original Kenwood "Dual Bander" concept. The wide range of innovative features includes a dual channel watch function, selectable full duplex operation, 30 memory channels, extended frequency coverage, large multi-color digital LCD displays, programmable scanning, and more!

- Extended receiver range (138,000-173,995 MHz) on 2 m; 70 cm coverage is 438,000-449,995 MHz; 1-1/4 m coverage is 215-229,995 MHz. (Specifications guaranteed on Amateur bands only. Two meter transmit range is 144-148 MHz. Modifiable for MARS/CAP. Permits required.)
- Separate frequency display for "main" and "sub-band."
- Call channel function. A special memory channel for each band stores frequency, offset, and sub-tone of your favorite channel. Simply press the CALL key, and your favorite channel is selected!

Optional Accessories:

- RC-10 Multi-function handset/remote controller • PS-430 Power supply • TSU-6 CTCSS decode unit • SW-100B Compact SWR/power/volt meter • SW-200B Deluxe SWR/power meter • SWT-1 2 m antenna tuner • SWT-2 70 cm antenna tuner • SP-400 Compact mobile speaker • SP-50B Deluxe

- 30 multi-function memory channels. 14 memory channels and one call channel for each band store frequency, repeater offset, CTCSS, and reverse. Channels "A" and "b" establish upper and lower limits for programmable band scan. Channels "C" and "d" store transmit and receive frequencies independently for "odd splits"
- 45 Watts on 2 m, 35 watts on 70 cm, 25 watts on 1-1/4 m. Approx. 5 watts low power.
- Automatic Band Change (A.B.C.) Automatically changes between main and sub-band when a signal is present.
- Dual watch function allows VHF and UHF receive simultaneously.
- Programmable memory and band scanning, with memory channel lock-out and priority watch function.
- Balance control and separate squelch controls for each band.

- Dual antenna ports.
- TM-621A has auto offset.
- Full duplex operation.
- CTCSS encode/decode selectable from front panel or UP/DWN keys on microphone. (Encode built-in, optional TSU-6 needed for decode.)
- Each function key has a unique tone for positive feedback.
- Illuminated front panel controls and keys.
- 16 key DTMF mic. included.
- Handset/remote control option (RC-10).
- Frequency (dial) lock.
- Supplied accessories: 16-key DTMF hand mic., mounting bracket, DC cable.

Complete service manuals are available for all Kenwood transceivers and most accessories. Specifications, features, and prices are subject to change without notice or obligation.



TM-721A shown with optional RC-10

- mobile speaker • PG-2N DC cable • PG-3B DC line noise filter • MC-60A, MC-80, MC-85 Base station mics. • MA-4000 Dual band 2 m/70 cm mobile antenna (mount not supplied) • MB-11 Mobile bracket • MC-43S UP/DWN hand mic. • MC-48B 16-key DTMF hand mic.

KENWOOD

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HAM RADIO

OCTOBER 1988

volume 21, number 10

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HAM RADIO Magazine is published monthly by
Communications Technology, Inc.
Greenville, New Hampshire 03048-0498
Telephone: 603-878-1441

subscription rates

United States:
one year, \$22.95; two years, \$38.95; three years, \$49.95
Europe (via KLM air mail), \$40.00

Canada, Japan, South Africa and other countries (via surface mail),
one year, \$31.00; two years, \$55.00; three years, \$74.00

All subscription orders payable in U.S. funds, via international
postal money order or check drawn on U.S. bank

International subscription agents: page 101

Microfilm copies are available from
Buckmaster Publishing
Mineral, Virginia 23117

Cassette tapes of selected articles from **HAM RADIO**
are available to the blind and physically handicapped
from Recorded Periodicals,
919 Walnut Street, Philadelphia, Pennsylvania 19107

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Second-class postage paid
at Greenville, New Hampshire 03048-0498
and at additional mailing offices
ISSN 0148-5989

Send change of address to **HAM RADIO**
Greenville, New Hampshire 03048-0498

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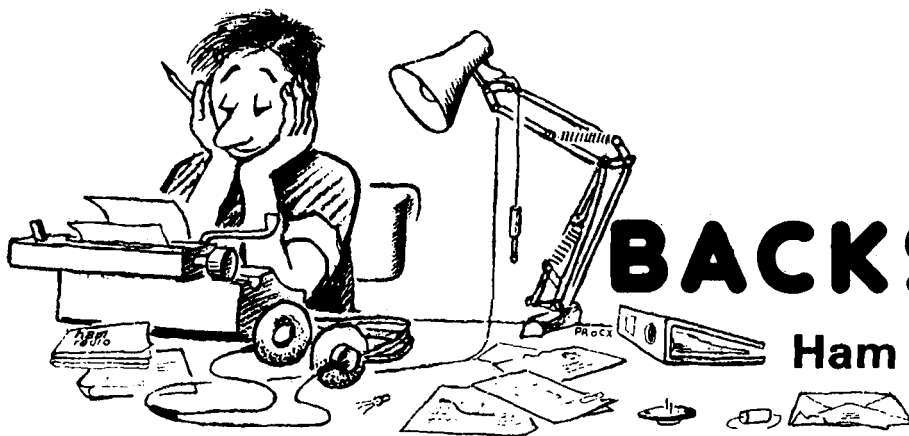


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WEEKENDER**

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BACKSCATTER

Ham Bands Under Siege?

Over the years, a number FCC actions have created a tremendous amount of controversy in the Amateur field.

The latest bombshell is assured of being one of the most hotly contested ever. On August 4, the FCC decided to reallocate 220-222 MHz to the Land Mobile Service. The roots of this action are in a proposal made 18 months ago by the FCC Office of Engineering & Technology to "address a need to promote spectrum efficient technology and reduce overcrowding in the commercial services." During the formal comments period, thousands of negative responses were filed by hams, concerned citizens, the military and other government services. In addition, Congressional resolutions against the proposal were working their way through both the House (Resolution -317) and Senate (Resolution -127).

Then from out of the blue, six months after the formal closing date for comments, the United Parcel Service, filed comments in support of the FCC proposal. Even more remarkable was the FCC's acceptance of the UPS proposal — it was as if they were prepared and had been waiting for it. Is the FCC saying to us now that the dates they put on proposals are flexible at the Commissioner's whims? One must wonder what kind of anarchy rules the FCC or where the pressure is coming from...

What's even more scary is the thought that this could only be the opening battle in the possible war to take away all of our frequencies. Chod Harris, editor of "The DX Bulletin" editorialized in the August 2 issue that due to lack of operation on the 30-meter band, it will only be a matter of time before another service proposes to take it away from us. There is the possible threat to 160 meters from the broadcasting industry. If they can move the band up to 1700 KHz, why not 1800 KHz, or even higher still? And what about 450 MHz? We've already lost part of the band on the Canadian border. What's to prevent a proposal to take all of the band from us based upon this action.

Now is the time to act. There are three ways you can help. First, write your congressional representatives and senators expressing support for the concurrent resolutions now before them. Second, the ARRL is urging all Hams to support a proposed amendment (see below) to legislation to freeze the FCC's rules as of August 3. Send your letters, telexes, QSLs in support of the amendment to Congressmen Markey and Dingle and Senators Inouye and Hollings at the addresses below. Finally, stay informed of all developments in this and all other actions that could seriously affect our hobby!

There's no turning back now! What couldn't happen has. If we do not stand up to this threat, who knows what we'll lose next.

Craig Clark, N1ACH

Radio Spectrum Allocation Amendment Spec. The Commission shall enforce the regulations, rules, and policies in effect as of August 3, 1988, as they relate to the Amateur Radio Service in the 220-225MHz frequency band as defined in 47 CFR Section 2.106 (Table of Frequency Allocations).

U.S. HOUSE

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Tel: (202) 225-4071
Attn: John Orlando

Rep. Edward J. Markey (D-MA)
Chairman of Telecommunications and Finance Subcommittee
Room 316, House Annex II
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Chairman Commerce, Science and Transportation
Room SD-508
Washington, D.C. 20510
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Attn: Ralph B. Everett

Sen. Daniel K. Inouye (D-HI)
Chairman of Communications Subcommittee
Room SH-227
Washington, D.C. 20510
Tel. (202) 224-9340
Attn: Tom Cohen

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NEW!

Affordable DX-ing!

TS-140S

HF transceiver with general coverage receiver.

Compact, easy-to-use, full of operating enhancements, and feature packed. These words describe the new TS-140S HF transceiver. Setting the pace once again, Kenwood introduces new innovations in the world of "look-alike" transceivers!

- Covers all HF Amateur bands with 100 W output. General coverage receiver tunes from 50 kHz to 35 MHz. (Receiver specifications guaranteed from 500 kHz to 30 MHz.) Modifiable for HF MARS operation. (Permit required).
- All modes built-in. LSB, USB, CW, FM and AM.
- Superior receiver dynamic range Kenwood DynaMix™ high sensitivity direct mixing system ensures true 102 dB receiver dynamic range.



- New Feature! Programmable band marker. Useful for staying within the limits of your ham license. For contesters, program in the suggested frequencies to prevent QRM to non-participants.
- Famous Kenwood interference reducing circuits. IF shift, dual noise blankers, RIT, RF attenuator, selectable AGC, and FM squelch.

- M. CH/VFO CH sub-dial. 10 kHz step tuning for quick QSY at VFO mode, and UP/DOWN memory channel for easy operation.
- Selectable full (QSK) or semi break-in CW.
- 31 memory channels. Store frequency, mode and CW wide/narrow selection. Split frequencies may be stored in 10 channels for repeater operation.
- RF power output control.
- AMTOR/PACKET compatible!
- Built-in VOX circuit.
- MC-43S UP/DOWN mic. included.

Optional Accessories:

- AT-130 compact antenna tuner • AT-250 automatic antenna tuner • HS-5/HS-6/HS-7 headphones • IF-232C/IF-10C computer interface
- MA-5/VP-1 HF mobile antenna (5 bands)
- MB-430 mobile bracket • MC-43S extra UP/DOWN hand mic. • MC-55 (8-pin) goose neck mobile mic. • MC-60A/MC-80/MC-85 desk mics.
- PG-2S extra DC cable • PS-430 power supply
- SP-40/SP-50B mobile speakers • SP-430 external speaker • SW-100A/SW-200A/SW-2000 SWR/power meters • TL-922A 2 kW PEP linear amplifier (not for CW QSK) • TU-8 CTCSS tone unit
- YG-455C-1 500 Hz deluxe CW filter, YK-455C-1 New 500 Hz CW filter.



TS-680S

All-mode multi-bander

- 6m (50-54 MHz) 10 W output plus all HF Amateur bands (100 W output).
- Extended 6m receiver frequency range 45 MHz to 60 MHz. Specs. guaranteed from 50 to 54 MHz.
- Same functions of the TS-140S except optional VOX (VOX-4 required for VOX operation).
- Preamplifier for 6 and 10 meter band.



Complete service manuals are available for all Kenwood transceivers and most accessories. Specifications, features, and prices are subject to change without notice or obligation.

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COMMENTS

Remembering a great scientist

Dear HR

KR6A in his article on Hertzian Waves omitted the findings of a very great scientist. I speak here of Nikola Tesla who proved that radio waves travel as do sound waves, i.e. longitudinally.

He also proved that Hertzian Waves are transverse waves and that these exist in the gases of the antenna both transmitting and receiving.

From this it can be seen that Hertzian Waves do not travel through space.

Arnold King, Jr. W2ZT, McAllen, Texas 78504

Neutral grounding

Dear HR:

Even though I'm very busy preparing for a vacation I feel compelled to write in reference to the excellent letter in the July issue (1988) of Ham Radio by I.L. McNally, K6WX and his subject of neutral grounding. The subject is especially timely, as that same issue carries an article by Bill Orr on page 60 and gives reference to grounding the neutral at an amplifier.

There are several additional reasons for grounding the "neutral" current

carrying conductor *only* at the service entrance; these are addressed in the National Electrical Code. One of the main reasons for grounding one of the secondary wires of the step-down transformer which supplies electricity from the distribution system is for safety. Should the transformer insulation fail and the secondary not be grounded by some means, that fault could put a very high voltage (7,000 volts or more) on house wiring, as measured to ground. But precautions must also be taken when the neutral is grounded. It is sort of a case where one solution somewhat creates another problem if proper wiring practice is not followed. The problem is that should the conducting path somehow be broken between the neutral bus between the load the transformer, and a small neutral wire somewhere in the house (say 14 g. for instance) be grounded, all neutral current (which could be 100 or 200A depending on the "unbalance") will flow over that 14 g. wire (which is normally rated at about 15A current capacity for house wiring) and possibly cause a fire. Then, yet another problem can occur. When the 14 g. wire melts through, the neutral will no longer be at ground potential depending on the load across the hot to neutral, and any equipment that is connected to what was once a neutral at something close to ground potential is now possibly somewhere near 120 v.a.c. creating a real shock hazard!

There is an important difference between a *grounding* conductor and a *current-carrying grounded neutral* conductor. In addition to the reasons listed above, any ground fault breaker or receptacle I have ever worked with will trip if its neutral is grounded anywhere downstream of the ground fault protector. Don't bypass ground fault protection or disable it in order to ground a neutral somewhere. *Don't ground neutrals* for important safety reasons, not to mention ground loops, hum, and rfi problems. Proper use of 240 v.a.c. and 120 v.a.c. in a device which requires both voltages demands

a four-wire system of two hot wires, the neutral grounded current-carrying conductor, and the grounding conductor; all the excuses ("it's my wiring, I'll do with it what I want; I don't believe in the wiring code; the government isn't going to tell me what to do,") notwithstanding, including what you see in radio handbooks. I also must politely and gently chastise Bill Orr for seemingly promoting this incorrect and dangerous practice. I suggest the proper wiring methods be addressed, with schematics, in one of his very next articles.

Richard M. Lorenzen, WA0AKG,
Lincoln, Nebraska 68504

Need for basics

Dear HR

As a long-time subscriber to your magazine, let me congratulate you on your announced intentions of changing the editorial policy with regard to the type of articles we can expect to find in *HAM RADIO*.

The quality of your articles in the past has been excellent for the better educated electronic engineer, but I find too many of the average hams are not able to cope with the math and other explanations. They look at the article and lay the magazine down without reading this type of article. Pretty soon they find so little use for the magazine, they drop the subscription. I have had considerable contact with many hams in this area and that is what they have given me to understand.

Many times hams have told me they got along fine building things with tubes but they got behind on semiconductors and now they are lost. It seems to me there is a need for articles stressing basic understanding of how semiconductors work and articles on building with simple standard transistors and ICs, not the latest sophisticated ICs that are not available to most hams.

I hope your change of policy works!

Robert R. Hall, W0CRO, Minneapolis, Minnesota 55406

MFJ 3 KW Roller Inductor Tuner

... lets you get your SWR down to *absolute minimum* -- something a tapped inductor tuner just can't do ...

... plus you get a *peak reading* Cross-Needle SWR/Wattmeter, 6-position antenna switch, balun for balanced lines and 1.8-30 MHz coverage...\$239.95



MFJ-986

\$239⁹⁵

MFJ's innovative new Differential-T Tuner™ uses a differential capacitor that makes tuning foolproof and easier than ever. It ends constant re-tuning with broadband coverage and gives you minimum SWR at only one setting.

The new MFJ-986 is a rugged no-compromise 3 KW PEP Roller Inductor antenna tuner that covers 1.8-30 MHz continuously, including MARS and all the WARC bands. The roller inductor lets you tune your SWR down to the *absolute minimum* -- something a tapped inductor tuner just can't do.

A 3-digit turns counter plus a spinner knob gives you precise inductance control -- so you can quickly return to your favorite frequency.

You get a lighted Cross-Needle meter that not only gives you SWR, forward and reflected power at a glance -- but also gives you a *peak-reading* function! A new directional coupler gives you even more accurate readings over a wider frequency range.

You get a 6-position ceramic antenna switch that lets you select two coax lines and/or random wires (direct or through tuner), balanced line and external dummy load.

A new current balun for balanced lines minimizes feedline radiation that causes field pattern distortion, TVI and RF in your shack. Ceramic feedthrough insulators for balanced lines withstand high voltages and temperatures.

New Antenna Tuner Technology
MFJ brings you three innovations in antenna tuner technology: a new Differential-T™ circuit simplifies tuning; a new directional coupler gives you more accurate SWR, forward and reflected power readings; and a new current balun reduces feedline radiation.

Differential-T Tuner™:
A New Twist on a Proven Technology

By replacing the two variable capacitors with a single differential capacitor you get a wide range T-network tuner with only two controls -- the differential capacitor and a roller inductor.

That's how you get the new MFJ Differential-T Tuner™ that makes tuning easier than ever, gives you minimum SWR at only one setting and has a broadband response that ends constant re-tuning. You'll spend your time QSOing

instead of fooling with your tuner.

The compact 10¼ x 4½ x 15 inch cabinet has plenty of room to mount the silver-plated roller inductor away from metal surfaces for maximum Q -- you get high efficiency and more power into your antenna.

The wide spaced air gap differential transmitting capacitor lets you run a full 3 KW PEP -- no worries about arcing.

A New Directional Coupler:
Accurate SWR and Power Reading

MFJ's Cross-Needle SWR/Wattmeter gives you more accurate SWR and power readings over a wider frequency range with no frequency sensitive adjustments.

That's because MFJ's new directional coupler gives you up to an order of magnitude higher directivity and coupling factor than conventional circuits -- plus it gives you a flat frequency response that requires no frequency compensation.

The cross-needle meter lets you read forward/reflected power in 2 ranges: 200/50 and 2000/500 watts. The meter lamp is front-panel switched and requires 12 volts.

A switch lets you select peak or average power readings.

A New Current Balun:
Reduces Feedline Radiation

Nearly all commercially built tuners use a "voltage" balun. The "voltage" balun forces the voltages to be equal on the two antenna halves. It minimizes unbalanced currents only if the antenna is perfectly balanced -- not the case with practical antennas.

The MFJ-986 uses a true current balun to force equal currents into the two antenna halves -- even if your antenna is not perfectly balanced -- so you get minimum unbalanced currents.

The current balun gives superior balance over the "voltage" balun.

Minimum unbalanced current reduces field pattern distortion -- which concentrates your power for a stronger

signal -- plus it reduces TVI and RF in your shack caused by feedline radiation.

The MFJ-986 Differential-T Tuner™:
Get *absolute minimum* SWR

Get the tuner that incorporates the latest innovations by the world's leader in antenna tuner technology.

See your dealer today for the new MFJ-986 Differential-T™ 3 KW Roller Inductor Tuner. Include \$10 shipping/handling if ordering direct.

WHY CHOOSE AN MFJ TUNER?

Hard-earned Reputation: There's just no shortcut. MFJ is a name you can trust -- more hams trust MFJ tuners throughout the world than all other tuners combined.

Proven Reliability: MFJ has made more tuners for more years than anyone else -- with MFJ tuners you get a highly-developed product with proven reliability.

First-rate Performance: MFJ tuners have earned their reputation for being able to match just about anything -- anywhere.

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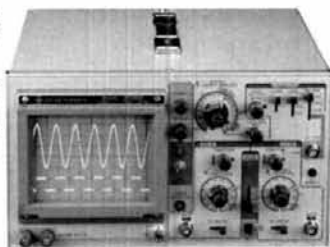
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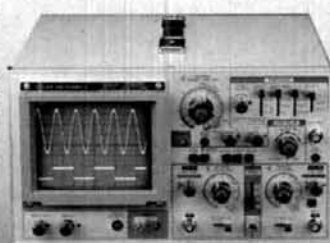


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EXPLORING PACKET RADIO WITH KISS

By Michael Pechura, WA8BXN, CIS
Department, Cleveland State University, E.
24th at Euclid Avenue, Cleveland, Ohio 44115

Learn more about
what you're sending
and how it works

Packet radio is one of the few areas left in Amateur Radio where you can do some experimentation with only a modest outlay for equipment. Those who already have a packet radio station have most of the equipment they need.

Unfortunately, most people on packet are "appliance" operators, not experimenters. I know it's easy to get on packet radio, but what do you do after connecting to all the locals on packet, reading all the messages on the bulletin boards, and watching all the Netrom "garbage" go by? Is there anything more you can do to find out about the real workings of packet, to experiment with this form of digital communication, and learn more about the interaction of your computer with packet radio? There certainly is!

There have been many articles explaining the data formats and the concept of networks, but it's also important to see packets in detail as they are being used. Fortunately, many of the Terminal Node Controller (TNC) manufacturers have begun to include a new feature in their TNCs, making experimentation and learning the details of packet easier. The feature is KISS mode (Keep It Simple Stupid!) access to the TNC. Provided to support a networking method called TCP/IP, KISS lets your computer do all of the decoding and construction of basic packet frames.

You can use KISS to really see everything in the packets being heard, and then to generate any type of packets you want. Now you can use your computer

to implement any new features you might like to put in your TNC.

There are some problems, however. With KISS you can transmit your own packets, but you shouldn't write anything to the TNC when you're in KISS mode until you fully understand the process. If you don't and send out packets with errors, they will probably be ignored by the TNCs receiving them. They also might be illegal, particularly if there isn't a valid identification transmission. Transmission of valid packets isn't really very hard, but it's important to listen and learn first.

To understand what happens in KISS mode you'll need to review what the TNC does when it's not in KISS. The TNC contains a microcomputer for the initial input of commands. When the connect command is given, the TNC transmits the right kind of packet to initiate a connection. If the connect request is successful, the lines you typed are made into packets to be transmitted. The packets received are sent to the computer to be displayed as lines of text. The TNC handles all the details of the AX.25 protocol, like sequence numbers and error handling. These details aren't important if you don't intend to experiment with packet radio.

When a TNC is running in KISS mode it receives a string of characters that make up the complete packet to be transmitted from the computer. When the TNC receives a packet it sends the whole thing to the computer, and the computer then decides what to do with it. The TNC sends all packets it hears to the computer and the computer must retransmit the lost packets. There is no command mode; the TNC acts much like a dumb modem. However, when the TNC is sent a packet to transmit, it is responsible for generating the proper error detection bits at the end of the packet. It also waits until the channel is clear before transmitting and keys the push-to-talk line. When the TNC hears a packet on the radio, it checks the error detection bits and ignores the packet if it contains an error.

The details of KISS mode

Because KISS mode is simple, the description of its interface is short. Once in KISS mode, strings of bytes are sent by the TNC to the computer for each packet it receives. The beginning and end of these strings are marked by bytes of **C0** hex. These strings are called frames and they all have this basic pattern: **C0 YY XX XX XX XX XX ... XX XX C0**

where **YY** is the type of KISS frame (normally 0 in frames from the TNC) and the **XX**'s represent bytes that form a packet. These bytes might be header information or data being transmitted in the packet. The first byte after **C0** is a command byte identifying the kind of frame. This byte will be 0 for data received from the TNC for single port TNCs.

A minor problem arises when a packet contains a byte that is hex **C0**. You must not confuse this **C0** with the one that marks the end of the packet, so the TNC will never send a byte that is within a packet with the bit pattern **C0**. If such a byte does exist it will send two bytes, **DB** and **DC**, indicating that a byte of **C0** is actually in the packet. This solution for the **C0** problem gives rise to another one — how to have the bit pattern **DB** in a packet. This is solved by never sending a byte that is part of a packet as **DB**. In its place two bytes are sent, **DB** followed by **DD**. The situation above is referred to as the transparency problem, or how to tell data from delimiters. (It's much like the programming question of how to put a quote mark in a character string that is enclosed in quotes.)

Frames sent to the TNC by the computer also use this same format, with some different values for the command byte. You must follow the rules carefully for solving the transparency problem given above. For the present, concentrate on what you can learn and do by just listening in KISS mode; don't worry about transmission details yet.

Programs for your computer

It isn't terribly difficult to write programs for KISS mode. They can be written in most languages. My favorite program language is C. BASIC is a much more widely available language, however, and the programs given here will use it.

Because the bytes from the TNC in KISS mode arrive at the computer at times determined by the TNC, the program running in the computer must be ready to receive them. *Interrupt driven serial I/O is required.*

Two popular computers for Amateur Radio are the C-64 and the IBM PC, and its clones. Because some of the syntax for BASIC is quite different for these two computers, I've provided listings for both machines. You can adapt the programs for your own machine. Interrupt driven serial I/O is standard in BASIC for the

C-64 and IBM PC. Make sure this is also the case for any other computer you might use.

Just about any TNC that supports KISS mode can be used with these programs. The difference between one TNC and the next is the set of commands used to get the TNC into KISS mode. The TNC used to prepare these programs is a Kantronics KPC-2, which can be used with either true RS-232 compatible computers or the TTL levels used by the C-64. When using another TNC, refer to its operating manual for the necessary commands.

The simplest (and sometimes most useful) program that can be written for KISS mode is one that displays, in hex, the bytes the computer receives from the TNC. This program lets you see everything there is in a frame, including the **C0** bytes at the beginning and end.

The program for the C-64 is listed below:

```
10 PRINT CHR$(147) + CHR$(5);:POKE 53280,0:POKE
   53281,0
20 OPEN 2,2,3,CHR$(7): GET# 2,A$
30 PRINT# 2,"KISS ON" + CHR$(13) + "RESET"
40 H$ = "0123456789ABCDEF"
50 GOSUB 100: A = ASC(A$)
60 PRINT MID$(H$,A/16 + 1,1) + MID$(H$,A AND
   15) + 1,1) + " ";
70 GOTO 50
100 IF PEEK(667) = PEEK(668) THEN 100
110 GET# 2,A$: IF A$ = "" THEN A$ = CHR$(0)
120 RETURN
```

Go through this program line by line noting the subtleties. This will help if you want to convert it to another version of BASIC. Line 10 uses a print statement to clear the screen with **CHR\$(147)** and set the character color to white with **CHR\$(5)**. There are single keystrokes that could be enclosed in double quote marks for these, but since they usually don't reproduce well in listings the equivalent **CHR\$** forms are used instead. The two **POKE** statements set the background and border colors to black. While these colors work best on my color monitor, you may change them if you prefer.

Line 20 opens the serial port as device 2. The 7 in the **CHR\$(7)** specifies 600 baud operation. The default of 8 data bits with no parity matches the format of data from the TNC when in KISS mode. Because 600 baud operation has been specified (the C-64 may not operate reliably at higher speeds), the TNC must also be set for 600 baud operation to the computer (**ABAUD 600** for the KPC-2 TNC). The **GET# 2,A\$** turns on the interrupt system. Any byte actually read at this time is discarded.

Line 30 sends commands to the TNC as if they had been typed during normal use of the TNC. "KISS ON" tells the TNC to turn on KISS mode. This actually happens when the TNC is reset. Using **CHR\$(13)** is the same as pressing the return key after typing KISS ON.

Next, "RESET" is sent to the TNC. Because there is no semicolon at the end of this print statement, BASIC also sends a return character to the TNC along with a line feed which the TNC ignores.

Line 40 initializes a string to the hexadecimal digits used later to display the bytes in hex.

Line 50 calls the input routine that gets one byte from the TNC as the character variable A\$. The decimal equivalent is also put in the variable A.

Line 60 prints the byte received in hexadecimal form by using the high and low order 4 bits of the bytes, each of which selects a character from the string H\$. This method is used to print a byte in hexadecimal as C-64 BASIC doesn't include such a function. After the two hexadecimal characters are printed, two blank characters are printed. A single blank could be used between the hexadecimal values instead, giving more values on a screen, but two blanks keep the values lined up in columns. You may change this as you wish. After a byte in hexadecimal has been printed, Line 70 goes back to get the next byte from the TNC.

Line 100 begins the byte input routine. It's written as a subroutine for convenience in later programs, but could be included where called in line 50 of this program because it is only called from one place.

Besides getting a byte from the TNC, this input routine overcomes two problems found in the use of GET# alone. The first is that GET# always returns immediately whether a character is available or not. Locations 667 and 668 are addresses of bytes in the input buffer of the interrupt routine. When these addresses are the same, no characters have been received. The loop of line 100 waits for a character to be received. The second problem with GET# is that it gives a null string, both when no byte has been received and when the byte received is all 0 bits.

Since a byte of all 0 bits is valid when dealing with KISS mode, line 110 replaces a null character string with a byte of all 0 bits. You can do this because at line 110 a byte has been received. Line 120 simply returns to line 50 with the received byte in A\$.

Output from this program might look like the following:

```

C0 00 92 88 40 40 40 40 00 AE
82 70 84 B0 9C 01 03 F0 4D 53
59 53 20 69 6E 20 4B 49 52 54
4C 41 4E 44 2C 20 4F 48 20 20
57 41 38 42 58 4E 2D 31 33 2F
42 20 20 57 41 38 42 58 4E 2D
31 2F 4E 20 0D C0 C0 00 9A C2
D2 D8 40 40 00 AE 82 70 84 B0
9C 01 03 F0 4D 61 69 6C 20 66
6F 72 3A 20 41 4C 4C 20 C0

```

Here there are two frames, each beginning and ending with C0. Because the C-64 uses a 40-column display, there will be only 10 bytes per line. To study the

output, run the program during periods of low activity. Pressing the RUN STOP key will halt the program and let you study what's on the screen. (By the way, don't attempt to modify the program to send the screen output to the printer. Interrupts on the C-64 are turned off when it's printing and this prevents bytes from being received properly from the TNC.)

The output may include a few initial bytes that aren't in KISS mode. This is simply output from the TNC before it was switched into KISS mode. Turn the TNC off to get it out of KISS mode.

The IBM PC version of the program is structured like the C-64 version:

```

10 CLS
20 OPEN "COM1:600,N,8,1,CS,DS,CD" AS 2
30 PRINT #2,"KISS ON" + CHR$(13) + "RESET" +
  CHR$(13);
40 H$ = "0123456789ABCDEF"
50 GOSUB 100: A = ASC(A$)
60 PRINT MID$(H$,A/16 + 1,1) + MID$(H$,A AND
  15) + 1,1) + " ";
70 GOTO 50
100 A$ = INPUT$(1,2)
110 RETURN

```

Each line performs the same functions it did in the earlier program. Although BASIC on the IBM PC does provide a function to convert to hexadecimal, it gives only one hex character for values between 0 and F. Because this would cause variations in the spacing of the output, the same method used to convert to hexadecimal in the C-64 program is used again.

The input subroutine that begins at line 100 is simpler in this version of the program, since the INPUT\$ function found in BASIC on the IBM PC does all you need it to do. The output from this program looks much like the output from the C-64 version, except that now there will be 20 hex values per line. It's also possible to substitute LPRINT for PRINT in line 60 to send the output to the printer.

Suggested modifications

Now that you can see all the bytes in the frames and have verified that the format is indeed as described, what next? You can get a copy of the format descriptions of the various packet types, and see how the bytes displayed fit these formats by decoding them by hand. You can also make modifications to let this program help decode the packets. Adding everything needed to fully decode packets results in a considerably longer program (about a page long). There are a few simple program changes that will allow you to see some of the content of the packets more easily.

Try substituting the following statements in the program. They will work in either version.

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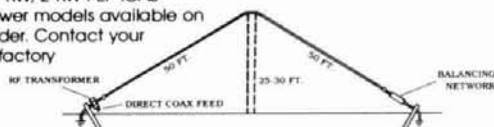
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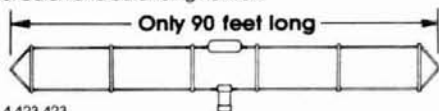
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```
60 IF A >= 32 AND A <= 126 THEN PRINT A$;
GOTO 50
65 PRINT " ";
```

These statements print as *characters* the bytes that are received from the TNC. Those that are normally unprintable will be displayed as dots. Quite a few funny-looking characters may be displayed, but you'll recognize some strings of characters that make sense. You should be able to recognize the text portion of the packets that would be seen if the TNC was being used normally.

Here's one output you might get while running on IBM PC:

```
....@@@...p.....MSYS in KIRTLAND, OH
WA8BXN-13/B WA8BXN-1/N.....@...p.....Mail
for: ALL .
```

Note that the spacing on the screen will be somewhat different. This output corresponds to the same bytes shown in the hexadecimal output examples above.

Another change that you can make follows. Again it will work with either version of the program.

```
60 A = INT(A/2):A$ = CHR$(A):IF A >= 32 AND
A <= 126 THEN PRINT A$;:GOTO 50
65 PRINT " ";
```

These changes will produce character output once again, but it will look different. You should be able to recognize the callsign portion of the packets (to and from callsigns and digipeaters, if any). The callsigns are shifted left 1 bit position in the packet, so the program makes them printable by shifting the bytes right 1 bit position (by dividing by 2). Sample output might look like this:

```
\.ID .WA8BXN..x&),).47.%$)*&'...'$. +
.\,.'... + .\.'...'
.\Mail .WA8BXN..x&046.379.. &&.'
```

Again, the output on the screen may be spaced slightly differently from what appears here in print. These are the same bytes, just looked at a different way.

Conclusions

These programs and their modifications should help you start using KISS mode to explore the details of packet radio. Anyone familiar with BASIC should be able to understand and modify the programs further.

Many improvements are possible; the possibilities are endless. Modifications can be made to monitor channel usage (Are the beacons really using up that much channel capacity?) or decode nonstandard packet types (What does all that "garbage" in Netrom packets really mean?). Here's a golden opportunity to experiment and put your computer and packet gear to good use when you're bored with just reading the mail.

Article A

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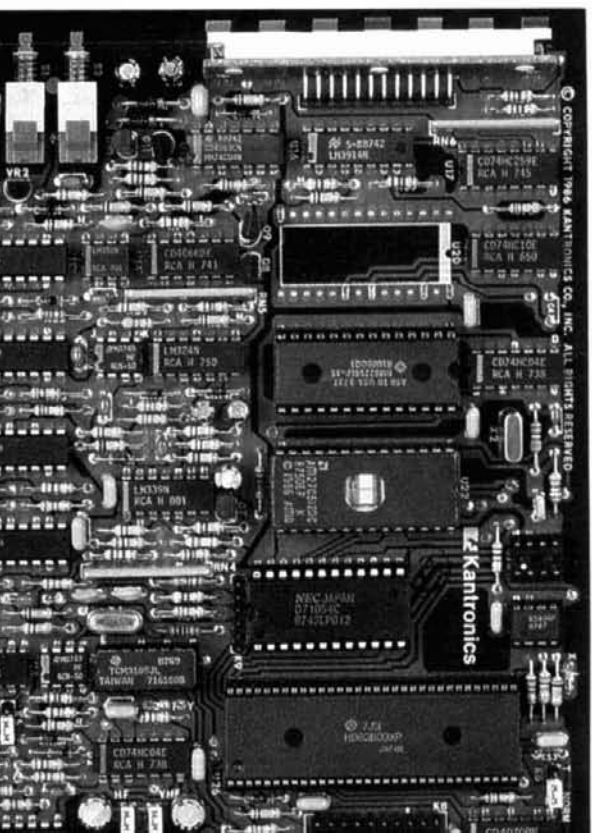
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FOR THE MICROWAVE BANDS: PART THREE

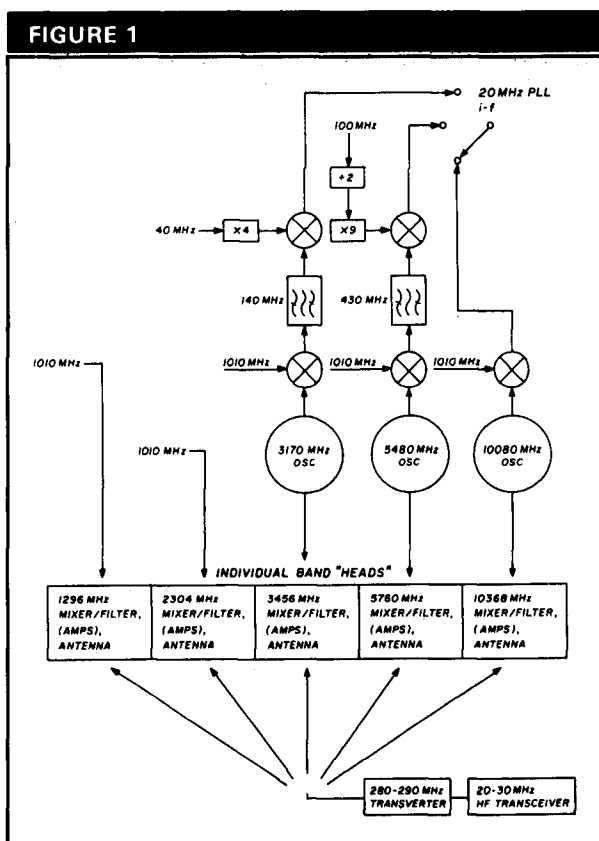
By Glenn Elmore, N6GN, 550 Willowside Road, Santa Rosa, California 95401

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station

Part 1 discussed some of the advantages micro-waves can have over lower frequency signals for point-to-point communications. I presented a generalized approach using phaselock techniques which allows access to the calling frequency on each Amateur microwave band and supports linear signal conversion: SSB, CW, and other narrowband modes. You can obtain a spectrally pure and precise local oscillator signal for any of the Amateur microwave bands with a single pc board design in several separate loops, including only those components needed for a particular loop. Table 1 in Part 1 showed that you can obtain SSB operation on all the Amateur bands from 1296-24192 MHz using a 1010-MHz reference oscillator to downconvert and phaselock an available microwave oscillator, along with an appropriate i-f and microwave signal mixer.

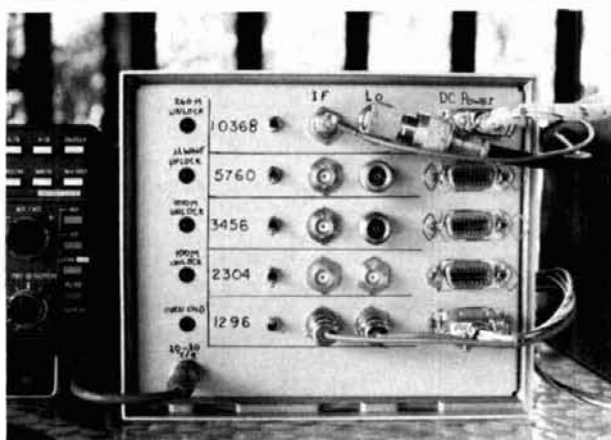
I've demonstrated this approach with the description of a 10368-MHz SSB station. But, its broader applications shouldn't be lost in the specifics of the 10-GHz example; the technique can be used with all of the microwave bands. You can achieve 1296-MHz, 2304-MHz, and 10368-MHz operation by adding the signal mixer/filters (a harmonic mixer with 1010-MHz LO drive can be used on 2304) once circuits for the 100-MHz quartz oscillator, 1010-MHz coaxial oscillator, and 10-GHz oscillator are functioning. Operation is possible at 3456 MHz and 5760 MHz with the addition of an oscillator/downconverter and signal mixer/filter. You can add more microwave amplification for transmit and receive on a band-by-band basis.

Although Table 1, part 1 showed how to get on all



Once the 10368-MHz station using the 280-290 MHz signal i-f is built, 1296 and 2304 MHz are immediately available. The two microwave bands in between, 3456 and 5780 MHz, may be included by adding suitable VCOs at 3170 and 5480 MHz, along with harmonic mixers and circuitry to convert their PLL i-f to 20 MHz.

PHOTO A



Five-band operation is easily obtained using this phaselocked transverter.

the bands using the 1010-MHz signal, some of the alternatives result in inverted tuning (high side LO) and a 432-MHz i-f. If you include a frequency conversion after the PLL harmonic downconverter, normal tuning and exclusive use of the 280-290 MHz i-f is feasible. **Figure 1** shows the block diagram for a five-band LO. You don't need to construct additional phaselock circuitry; you can use the 10-GHz phaselocking circuits for multiple bands as long as you provide similar oscillator tuning sensitivities. To change bands, simply switch the power and PLL i-f to the desired oscillator/downconverter. **Photo A** shows a phaselocked transverter with provision for five bands, having little more circuit complexity or size than previous single-band units.

You can get immediate 10368-MHz SSB operation if you have a 148-MHz transceiver and proper reference frequency to give a 10220-MHz LO. However, you'll need a 280-290 MHz i-f to take advantage of the potential multiband operation. Part 3 shows the circuits for the 260-MHz phaselocked oscillator, and the amplifier and switching circuits used to convert a 20-30 MHz Amateur transceiver to and from the 280-290 MHz intermediate frequency required for multiband microwave operation. I'll also show the two-stage GaAsFET amplifier used for the 10368 station.

260-MHz local oscillator

I'll begin the description of 280-290 MHz transverter with the 260-MHz phaselocked LO. It would have been easy to use a conventional approach because this transverter isn't very different from a low power (zero dBm) 220-MHz one. I could have used an 86.666-MHz crystal oscillator followed by a tripler and appropriate filtering, but I didn't want to compromise the frequency accuracy of the microwave station with a less

accurate unlocked i-f transverter LO. You can maintain overall frequency control by the 10-MHz frequency standard (or the 100-MHz crystal if it's operated unlocked) by using another common phaselock board and building a VCO at 260 MHz.

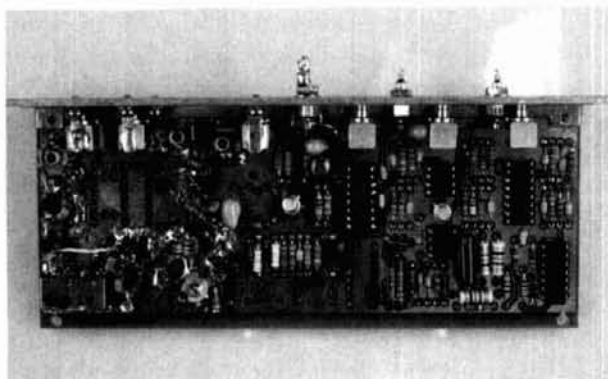
Obtain the 40-MHz PLL i-f by mixing the VCO output with the third harmonic of a 100-MHz reference signal. A standard double-balanced mixer (like an SRA-1) works well because it's effectively an odd harmonic mixer. A harmonic downconverter produces an appropriate i-f for locking. The oscillator uses a junction FET. (I make no claim that it's the best that can be done.) It isn't necessary to have superlative spectral purity in this application because, unlike the 1010-MHz case, no higher harmonics are used for further phaselocking; simplicity of design and ease of construction win. Even so, the spectrum of this LO when locked is good, and doesn't contribute significantly to microwave signal phase noise. The 260-MHz bandpass filters and buffer stages are present only for isolation and to keep any reference frequency derivatives from showing up on the 260-MHz signal. If you take care to separate the PLL i-f signals from the main 260-MHz output, any spurious signals are at least 75-dB down. **Photo B** shows the oscillator.

You'll need a 40-MHz reference frequency to lock this oscillator. A 20-MHz ECL reference signal drives a bipolar transistor frequency doubler, which drives an extra ECL line receiver. These circuits are located on the previously constructed 100-MHz reference board.

As with the 1010-MHz downconverter circuit, a 100-MHz bandpass filter and amplifier keeps any lower frequency signals on the ECL output from passing straight into the PLL i-f amplifiers through the harmonic mixer.

All of the locking circuits are identical to the ones used before. **Table 2**, part 1 shows component values for the loop filter. Component values for the lowpass

PHOTO B



This oscillator is used in obtaining the 260-MHz LO.

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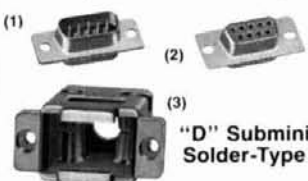


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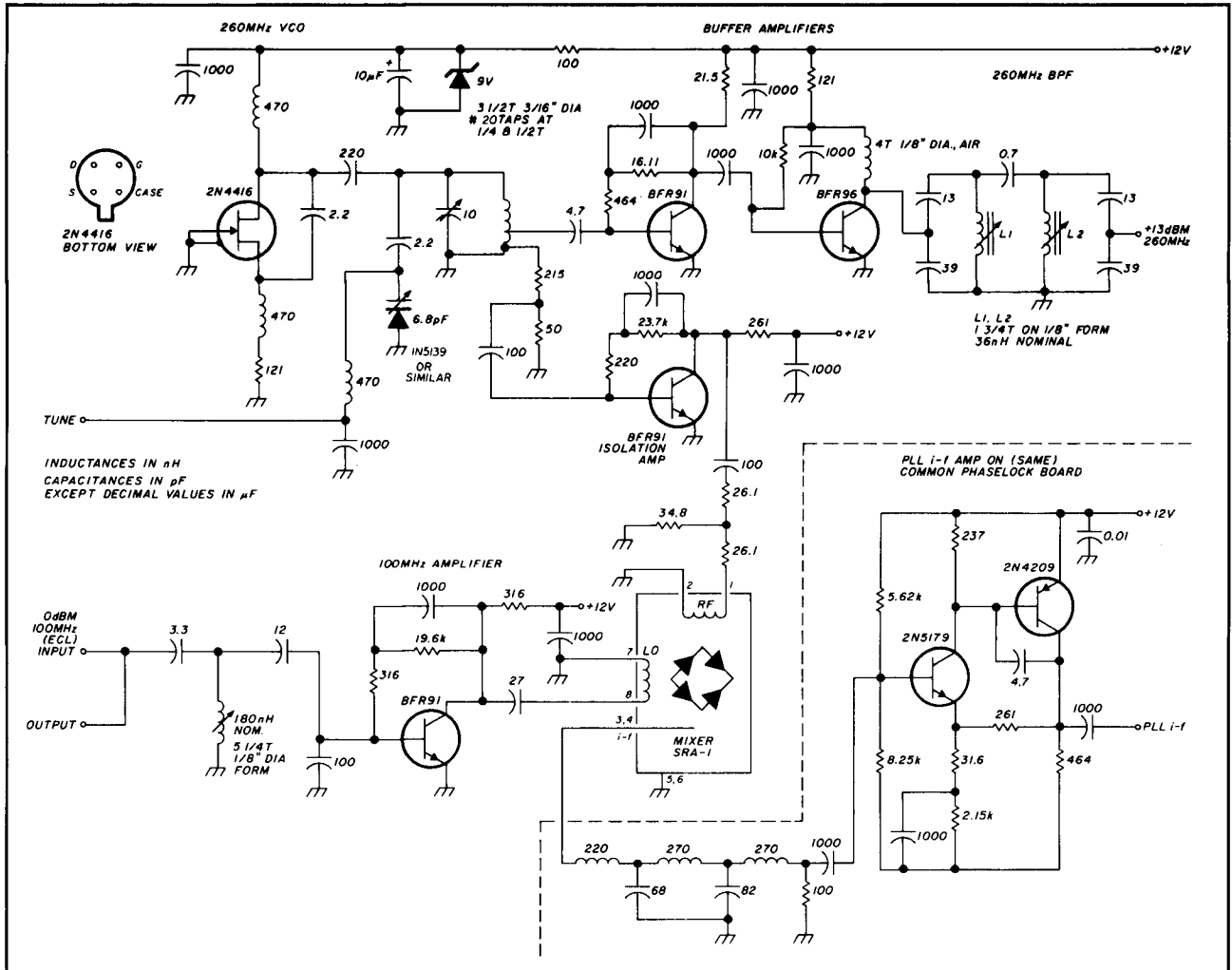
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FIGURE 2



The 260-MHz phase-locked LO for the 280-290 MHz transverter uses a simple junction FET oscillator and two different amplifiers — one for the signal mixer and the other for driving the harmonic downconverter.

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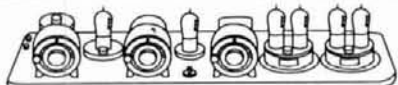
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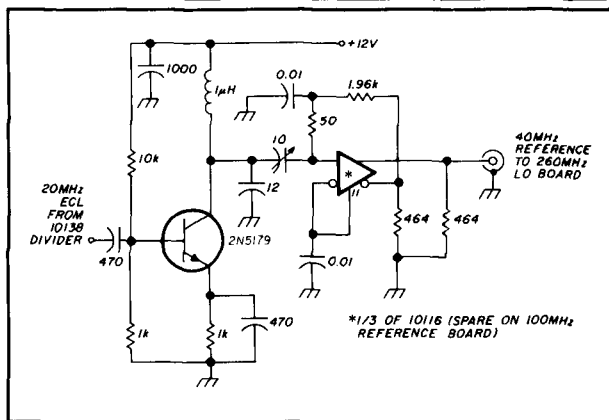
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FIGURE 3



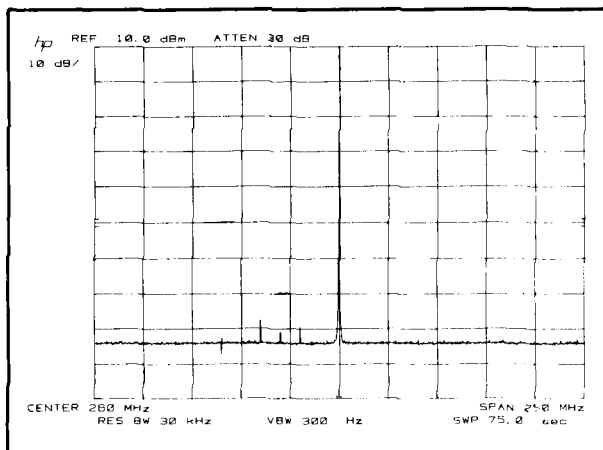
The 260-MHz locking circuitry requires a 40-MHz reference frequency. This is obtained by doubling the existing 20-MHz ECL signal in a transistor and restoring ECL logic levels with an extra 10116 line receiver.

filter after the harmonic mixer are modified to pass the 40-MHz PLL i-f. Use the jumpers marked "-" on the common phaselock board. Figure 2 shows the schematic of the oscillator/amplifier and PLL i-f. The 40-MHz reference circuit is shown in fig. 3. Figure 4 shows the spectrum of the phaselocked 260-MHz oscillator.

280-290 MHz transverter mixer, amplifiers, and switching

Figure 5 shows a block diagram for the 280-290 MHz transverter, fig. 6 is the schematic diagram and fig. 7 shows the dc biasing scheme. I tried to use easy to find parts and a design requiring a minimum of test equipment for final tuning. Broadband amplifiers are used in the hf and VHF portions of the transverter.

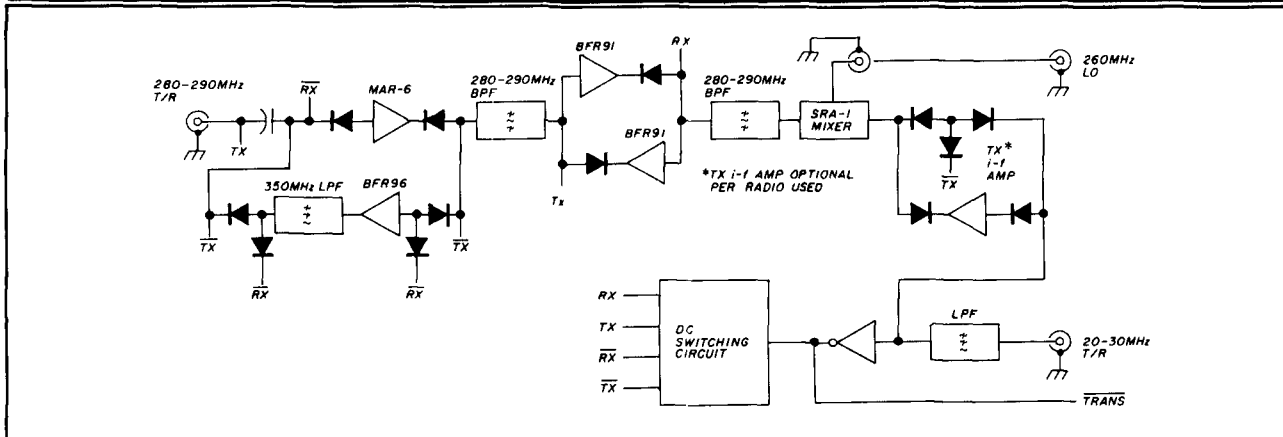
FIGURE 4



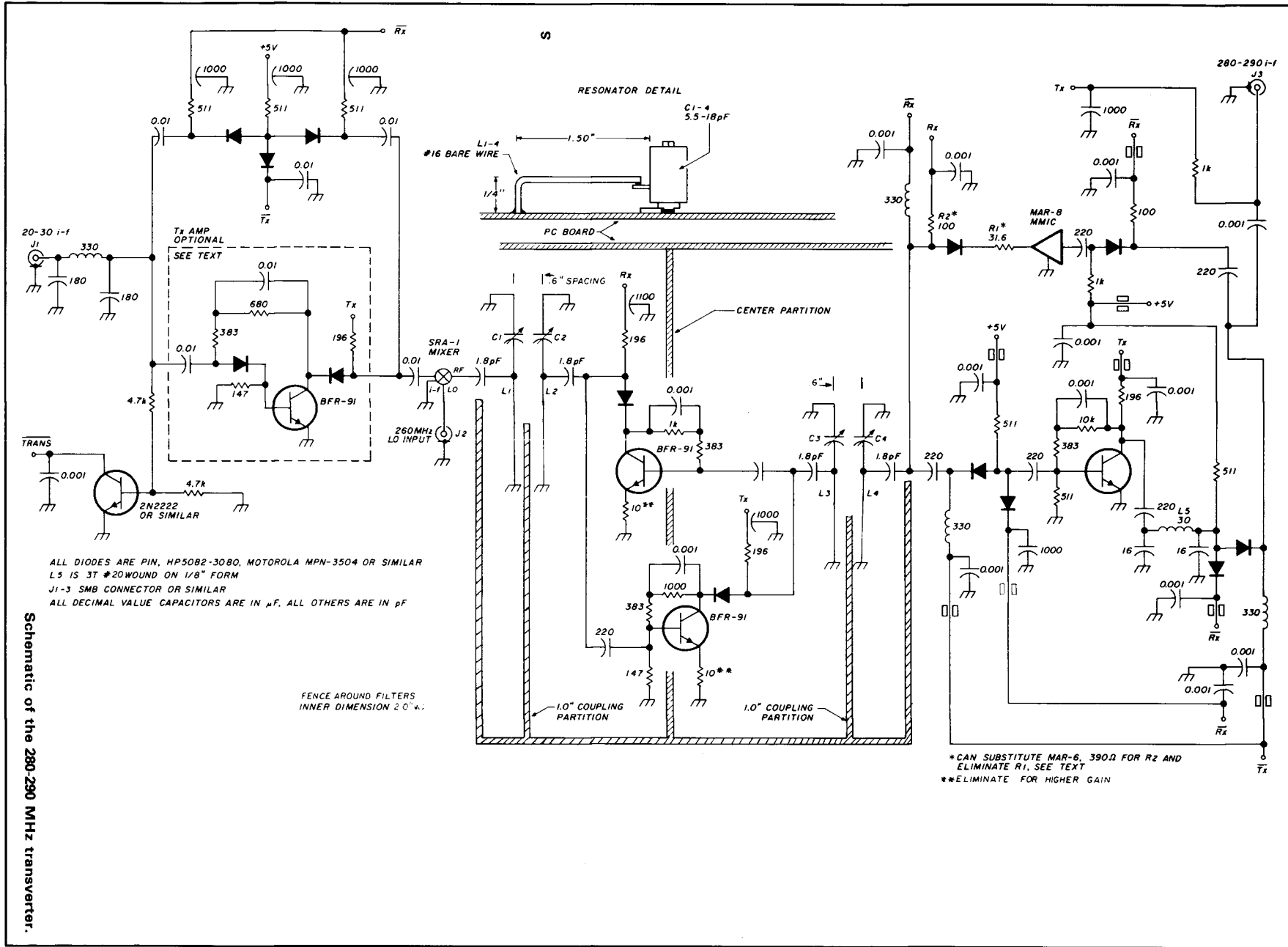
The spectrum resulting from phaselocking the 260-MHz VCO is quite clean. Both spurious signals and noise are small compared to the carrier.

Frequency selection is performed with a lowpass filter at hf and two 2-resonator filters for VHF. It's desirable to have a moderately high-gain low noise input stage to set the overall noise figure on receive at VHF. I chose an MMIC since Avantek/Mini Circuits MMICs seem to be easy to find at reasonable prices. I tried a MAR-8 (Avantek MSA-0885) first, and got good performance after taking care with grounding and construction techniques. To increase stability, I used a 30-ohm resistor in series with its output. The MAR-8 doesn't have heavy internal feedback to control its gain (and SWR), and provides a noise figure in the area of 3 dB. But this device is only conditionally stable and has *lots* of bandwidth — several GHz of it. You must control feedback paths as well as source and load impedances over a very large frequency range in order

FIGURE 5



The transverter uses a conventional double balanced mixer, broadband amplifiers, and appropriate filtering to convert the 20-30 MHz hf transceiver to 280-290 MHz. Transmit/receive switching is performed by PIN diodes and a dc switching circuit, which provides bias for the appropriate stages. Transmit output power of about 0 dBm (1 milliwatt) and receive conversion gain of about 8 dB is provided.



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Schematic of the 280-290 MHz transverter.

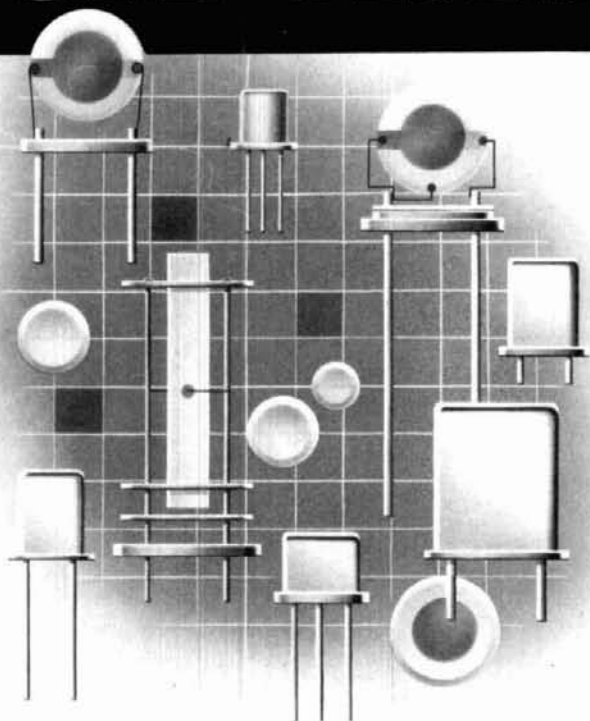
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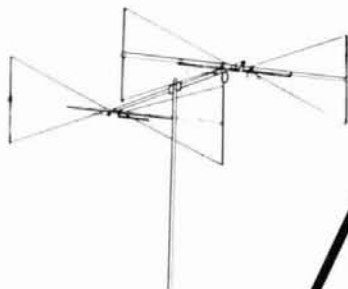
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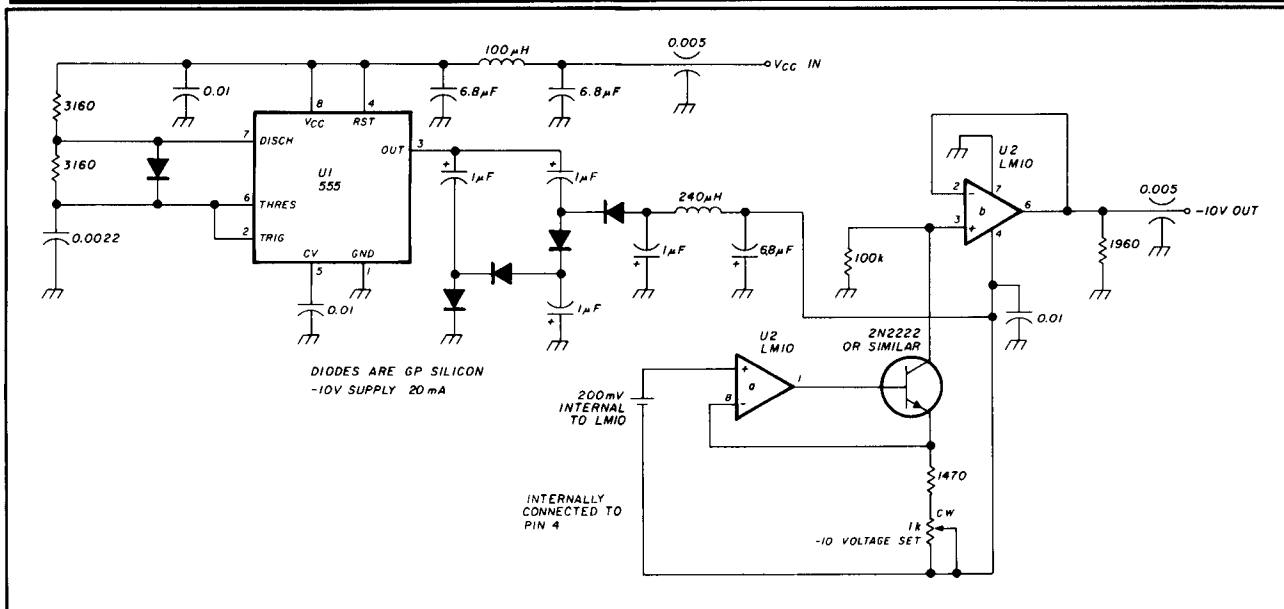
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FIGURE 7

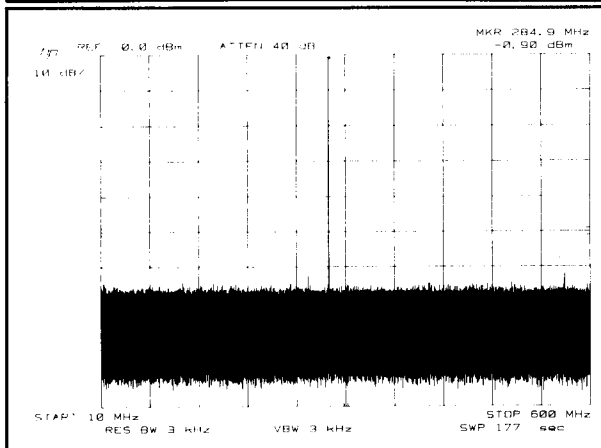


DC biasing scheme for the 280-290 MHz transverter.

to keep it from oscillating. I replaced the MAR-8 with a MAR-6 (Avantek MSA-0685) and got a better match. The MAR-6 is unconditionally stable, with better input and output match. This is important because the 280-MHz filter, if not the microwave signal mixer, requires low SWR terminations for minimum ripple and insertion loss. However, the MAR-6 has lower gain at 280 MHz than the "resistor stabilized" MAR-8. This results in a 0-3 dB conversion gain for the transverter with the MAR-6, in contrast to about 8 dB with the MAR-8. The extra gain with the MAR-8 helps the noise figure by overcoming the 280-MHz filter losses and interstage amplifier noise figure. Measured overall, transverter noise figure is about 3 dB with the MAR-8 and 5 dB with the MAR-6. If you use signal frequency amplifiers, and not just a "barefoot mixer", the lower conversion gain and higher noise figure of the MAR-6 may not be a concern. If you choose a MAR-6, change the collector bias resistor to 390 ohms and remove the 30-ohm series resistor required for the MAR-8.

I use a BFR-96 on transmit, with the appropriate collector and feedback resistances, to provide a compromise of gain and match at 280-MHz. This stage only needs about zero-dBm output to drive the signal mixer (assuming microwave LO power in the +10 dBm vicinity). The interstage amplifiers used between the two filter portions ensure a good input and output match for the filters to work against. I could have used a 4-resonator filter without interstage amplifiers instead of twin 2-resonator sections, but I felt that tuneup without test equipment would be harder. The mixer should probably look into a broadband 50-ohm

FIGURE 8



The spectrum of this transverter on transmit shows unwanted signals suppressed by more than 60 dB. At full output of about 0 dBm only the 280-MHz LO feedthrough and the second harmonic of the signal are visible.

termination instead of a filter for best signal performance and lowest conversion loss, but once again simplicity won out. Unwanted LO leakage and image signals should be at least 60-dB below maximum output. Figure 8 shows the output spectrum of the transverter on transmit.

For transmitting, special circuit versatility is necessary in the transverter's hf circuit. This is because there's no standard transvert-mode output power level for modern multiband Amateur transceivers. Some manufacturers provide outputs of 1-100 milliwatts, while others are almost 30 dB less. I used another BFR-

91 stage which can be "programmed" for various gains. The values on the schematic are right for my ICOM IC-751; it puts out about -15 -dBm maximum on SSB/CW transmit in transverter mode. If your exciter has more drive than this, you may need to eliminate the stage or put in a resistive attenuator. As shown, the transverter puts out about 0 to $+3$ dBm on voice peaks of my IC-751. The PIN diode switch lets the full mixer output reach the receiver during receive. If your station receiver has particularly low gain, you could include another amplifier stage here. This shouldn't be necessary for most applications using microwave preamplifiers. Even with a "barefoot mixer", the transverter as shown exhibits 8-10 dB conversion gain on receive. This should make up for most of the conversion loss from a microwave mixer.

The 280-290 MHz filter was designed to be easy to use and construct. The inductor is an extremely simple and reproducible wire-over-ground plane. I was concerned that most of the coupling between resonators might be between the tuning capacitors themselves, and too dependent upon construction technique and layout. However, construction with a number of different types of tuning capacitors produced similar results.

Other possibilities

Because this filter is the only block (besides the LO) which controls frequency, you should be able to obtain transverters for 144, 220, and 432 MHz by changing the filter elements. This might be attractive at 220 MHz as a frequency doubler driven by the 100-MHz reference could provide the LO. A 120-MHz phaselocked VCO with a 100-MHz downconverter reference and 20-MHz PLL i-f would work for 144 MHz. The downconverter could be a conventional mixer. A fourth-harmonic anti-parallel diode mixer with 100-MHz reference and 10-MHz PLL i-f would suffice to lock a 410-MHz VCO for 430-440 MHz operation.

Switching

Because of the number of possible bands, I devised a standard transmit/receive interface — each with its own microwave head (mixer, filter, amplifiers and T/R switch). You should get full microwave output power on transmit, with zero dBm of i-f power. I chose to use Vcc on the rf signal line to indicate transmit; this allows "daisy-chaining" control. When the hf transceiver signals transmit by pulling the NOT-transmit line low or putting Vcc on its signal line, the 280-MHz transverter amplifiers are turned on in the transmit direction, and Vcc is passed to its rf port. As a result, the connected microwave circuitry goes into transmit. For this reason, hardware for each microwave band can be located at, or near, the antenna, minimizing

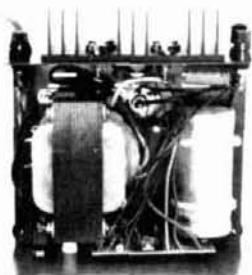
feedline losses. Any band can now be selected from the operating position by connecting the i-f from the transverter. The local oscillator signals incur power losses on the way to the heads. But, excess LO power is generally available and microwave signal mixer conversion efficiencies aren't much influenced by moderate reduction of LO drive, as long as LO power is several dB greater than the maximum i-f power of zero dBm. Even at 10 GHz where losses are greatest, you can probably locate the microwave head and antenna at least 10-20 feet from the operating position if you use good quality coax. All that's required between the operating position and the head for each band is the connection of two coaxial cables, i-f and LO, and one dc power cable (where needed). This allows for continuing enhancements in the microwave heads, improved noise figure, and higher power amplifiers — without the necessity of impacting the local oscillator sections. Feedhorn/head combinations can be quickly exchanged using a single antenna during a band-change, if you provide a mount for a standard box at the *feedpoint of a reflector antenna*.

Because the 280-MHz transverter is electronically switched, transmit turnaround time should be that of the hf transceiver alone — unless there is a slower mechanical T/R switch in the microwave head. Microwave AMTOR should work with this arrangement.

Although Vcc may be indicated as 12 volts on some of the previous schematics, I actually run the entire station from the output of a low-dropout 3-terminal adjustable regulator set to *11 volts*. This tends to keep gains and amplitudes stable, and allows operation on nearly discharged 12-volt automotive batteries. A separate 5-volt regulator provides the power for the ECL logic.

Transverter construction

I built the 260-MHz VCO in the space on the common phaselock board allocated for the 100-MHz oscillator and divider circuits. Because the board was made with lots of component-side ground plane, I soldered right to the ground plane or mounted components by their leads. Lead length was kept to a minimum. To do this, use 1/8th or 1/16th-watt resistors, and other physically small components. (I find that a large pair of tweezers is a great construction aid.) The lower impedance of the broadband amplifier stages tends to make them less sensitive to parasitic capacitances, which can be layout and lead-length dependent. Be particularly careful to connect directly the ground end of the capacitors and the coils on the 260-MHz band-pass filter. A clean, phaselocked $+10$ dBm 260-MHz signal results if the phaselock downconverter and 260-MHz amplifier/filter portions are kept at a reasonable distance from one another.



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RM-12M	9	12	5 1/4 x 19 x 8 1/4	16
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RM-50M	37	50	5 1/4 x 19 x 12 1/2	50

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RS-4A	3	4	3 3/4 x 6 1/2 x 9	5
RS-5A	4	5	3 1/2 x 6 1/4 x 7 1/4	7
RS-7A	5	7	3 3/4 x 6 1/2 x 9	9
RS-7B	5	7	4 x 7 1/2 x 10 1/4	10
RS-10A	7.5	10	4 x 7 1/2 x 10 1/4	11
RS-12A	9	12	4 1/2 x 8 x 9	13
RS-12B	9	12	4 x 7 1/2 x 10 1/4	13
RS-20A	16	20	5 x 9 x 10 1/2	18
RS-35A	25	35	5 x 11 x 11	27
RS-50A	37	50	6 x 13 1/4 x 11	46

RS-M SERIES



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• Separate volt and Amp meters				
RS-20M	16	20	5 x 9 x 10 1/2	18
RS-35M	25	35	5 x 11 x 11	27
RS-50M	37	50	6 x 13 1/4 x 11	46

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VS-12M	9	5	2	12	4 1/2 x 8 x 9	13
VS-20M	16	9	4	20	5 x 9 x 10 1/2	20
VS-35M	25	15	7	35	5 x 11 x 11	29
VS-50M	37	22	10	50	6 x 13 1/4 x 11	46
• Variable rack mount power supplies						
VRM-35M	25	15	7	35	5 1/4 x 19 x 12 1/2	38
VRM-50M	37	22	10	50	5 1/4 x 19 x 12 1/2	50

RS-S SERIES



MODEL RS-12S

- Built in speaker

MODEL	Continuous Duty (Amps)	ICS* Amps	Size (IN) H x W x D	Shipping Wt. (lbs.)
RS-7S	5	7	4 x 7 1/2 x 10 1/4	10
RS-10S	7.5	10	4 x 7 1/2 x 10 1/4	12
RS-12S	9	12	4 1/2 x 8 x 9	13
RS-20S	16	20	5 x 9 x 10 1/2	18

The 280-290 MHz circuits are built using a similar technique. But, for this board I started with a bare piece of approximately 3" x 6" double-clad 1/16th-inch thick Fiberglas™ pc board material (G-10). I cut 0.100" square pads and soldered all rf components to the board instead of building much of the circuit above the ground plane, as I did with the 260-MHz oscillator. Cutting out pads is easier than it sounds. You can prepare the entire board in one sitting with a microscope. Use a small hobby knife to cut away the copper around the pads. You'll get an isolated pad by scoring through the copper, then shifting the blade and cutting a vee or trough into the top of the board around a 0.100" square. As with the 260-MHz oscillator, the small component and pad size force you to control and limit the lead length. All ground connections should first be drilled completely through the board in the MMIC area. Then solder the component or lead to be grounded on both the top and bottom, to reduce the possibility of coupling inside the board. I drilled holes to clear the packages of the MMIC and the output BFR-96 transistor. This let me solder the emitter leads to the topside ground without excess lead length. Drill a hole for these leads and solder them to the top and bottom ground planes.

Be sure to follow the dimensions when making the filter inductors and mounting the tuning capacitors. The spacing between resonators in each pair is important to set filter coupling and provide the correct 8-10 MHz bandwidth. After cutting the pads and building the interstage amplifiers, solder the pc board "fence" on both sides around the filter assembly. The hf circuitry isn't critical, but I used the same "mini-pad" technique. It's desirable to connect the 260-MHz LO signal to the mixer with a piece of small coax. Try to use coax with an O.D. of 1/8" or smaller. Use minimum length on both the mixer and connector ends to avoid radiating 260-MHz energy around the filter, where it may be amplified during transmit by the output BFR-96. Such radiation could cause the unwanted LO feedthrough to be suppressed by less than 60 dB. This radiation would be in-band and small on all of the microwave bands, but it's unnecessary.

I built the dc switching circuits on a piece of breadboard, which I mounted at one end of the transverter. I suggest using a 0.125-A fuse or foldback current limiting in the dc supply until you've finished troubleshooting and tune-up because the PNP transistors will self-destruct if their cases, or the RX or TX supply lines are inadvertently shorted when they are turned on. In normal operation, all these transistors are used as switches and have very little power dissipated. I brought out the NOT-Transmit line to allow keying when an hf transceiver providing Vcc on the signal line during transmit is unavailable. This point

may also be monitored to tell if the hf transceiver is successful in causing the microwave station to go into transmit mode.

260-MHz LO tune-up

Finish the 260-MHz LO first; you'll use it to make the 280-290 MHz circuits work. Check your wiring and measure the current to the oscillator and each amplifier stage individually. As with the other loops, the phaselock portion, from the bipolar i-f amplifier onwards, can be checked by substituting one of the previously completed loops. A moderately sensitive detector of 40-MHz energy is desirable to tune the downconverter. An oscilloscope or a 40-MHz receiver should work. If you have neither, tune the oscillator to 271 MHz by listening to the PLL i-f at 29 MHz with the station receiver, to the PLL i-f at 29 MHz and tuning the variable capacitor slowly through its range. Do this with 6 volts applied to the tuning input. Verify that the signal heard tunes with the correct sense, and that you aren't overloading the receiver. Once you hear a signal which tunes correctly, peak it by adjusting the 100-MHz bandpass filter. To verify that the 40-MHz reference signal is present, use the diode detector from part 2, an oscilloscope, or other detector. To maximize it, peak the bipolar frequency doubler's collector tuning. Once the reference and PLL i-f inputs on the ECL phase comparator are at the correct level, the loop should lock when the VCO is (re)tuned to near 260 MHz. If you have trouble getting a sufficient level on the PLL i-f, temporarily bypass the attenuators on the input and output of the isolation amplifier to increase signal levels. It may be useful to count the VCO and keep track of operation during tune-up if a VHF frequency counter is available. Once the oscillator locks correctly with both isolation amplifier attenuators connected, peak the 260-MHz output by tuning L1 and L2 on the 260-MHz bandpass filter. You should now have a clean and accurate 260-MHz LO.

280-290 MHz tune-up

After completing rf circuit construction and re-checking the wiring, apply Vcc to each of the active stages with the switching circuitry disconnected. Measure and verify proper collector or emitter current. Verify that the TX, RX lines, and their complements alternate appropriately between nearly Vcc and ground as the TRANS line is alternately shorted to ground and allowed to float.

Once individual stage biases are correct and the switching circuits are functioning, complete the transverter construction by wiring the switched lines to the rf circuits. The transverter is probably best tuned on receive by using a local signal source in the 280-290 MHz range. The second harmonic of a 2-meter trans-

ceiver may be used, or the tenth of a 10-meter transmitter. Hook up the 260-MHz LO and the station receiver to the transverter. When you identify a suitable test signal, couple it to the bandpass filter nearest the interstage amplifiers on the MMIC side (280-MHz signal connector side). Tune the pair of resonators on the mixer side for maximum response. Next, couple the signal at the MMIC output side of the filter assembly and peak the other two resonators for maximum. The transverter should now be roughly tuned and operate on both receive and transmit. You can perform fine tuning to flatten the response over the full 10-MHz range by peaking one of the resonators in each pair on a 281-MHz signal and the other on a 289-MHz signal. If a 1290-1300 MHz transceiver is available, generate these i-f signals by connecting the 1010-MHz oscillator to a double-balanced mixer filter and completing the 1296-MHz station. The Mini-Circuits SBL-1X or TFM-2 mixers are only rated to 1 GHz for full specifications, but still perform reasonably well at 1296 MHz. If you use this method, you can tune up the transverter on either transmit or receive.

10-GHz amplifier

This two-stage amplifier was the next logical step in station improvement. Low noise amplification ahead of the mixer is necessary to reduce the overall receiver noise figure on receive. Without it the noise figure is approximately: $N_{F_{rx}} = N_{F_{if}} + C_{E_{mix}} (+ 3 \text{ dB})$.

Where:

$N_{F_{rx}}$ = receiver noise figure in dB

$N_{F_{if}}$ = 288-MHz i-f receiver noise figure in dB

$C_{E_{mix}}$ = conversion loss of the microwave signal mixer

Even with an amplifier you get the additional 3 dB because, unless an image reject signal mixer is used, the noise at the image frequency is converted to the i-f and degrades the overall noise figure. The system noise figure can be essentially that of the amplifier alone by providing sufficient gain ahead of a bandpass filter which passes only the signal frequency and not the image. On transmit it's desirable to have more power than the few hundred microwatts the mixer alone can achieve; gain is required to do this. Amplifier gain is worth more than low noise figure because it overcomes other hardware noise figure problems on receive, and directly adds to output power on transmit. This can mean 2-dB of station improvement for every extra dB of amplifier gain. For these reasons, the amplifier was designed to have a compromise of good noise figure and maximum gain.

Design considerations

Neither low noise or high gain are as easy to achieve at 10 GHz as at lower frequencies. Gallium Arsenide

field-effect transistors are currently the most readily available and suitable devices. Recent volume production of 4-GHz TVRO equipment has helped reduce the price and improve the performance of these parts. Gain elements aren't the only problem — losses in all circuit components whether lumped (like chip capacitors), or distributed (like microstrip transmission lines), must be kept to a minimum. Another significant problem (though not as noticeable at lower frequencies) is radiation loss. Wires, lines, and connections are no longer small in terms of the signal wavelength. Unless you take care to avoid it, a circuit can look more like an antenna than an amplifier. Building a circuit on a 2-1/2" long circuit board at 10.368 GHz is comparable to building one on a full-size football field at 40 meters. Packaging circuits at these frequencies can be a challenge since cavities and resonances resulting from mechanical dimensions can cause unexpected results. Can you imagine connecting one end of a coupling capacitor to a goal post and the other to the 20-yard line?

I chose a NEC NE-710 for the input stage and a NE-720 (or 2SK571) for the second stage. The 710 has lower noise and higher gain, while the 720 is relatively inexpensive. The 2SK571, which may only be available in Japan, is a bargain at about 500 Yen (\$4 US) on the surplus market there. The 710 is matched and biased for near minimum noise figure while the 720 is matched for maximum gain.

About 6 of these amplifiers have been built. Consistency has been good with "tuned" gain between 15.5-17 dB and noise figure between 2.6-2.9 dB at 10368 MHz, for the group.

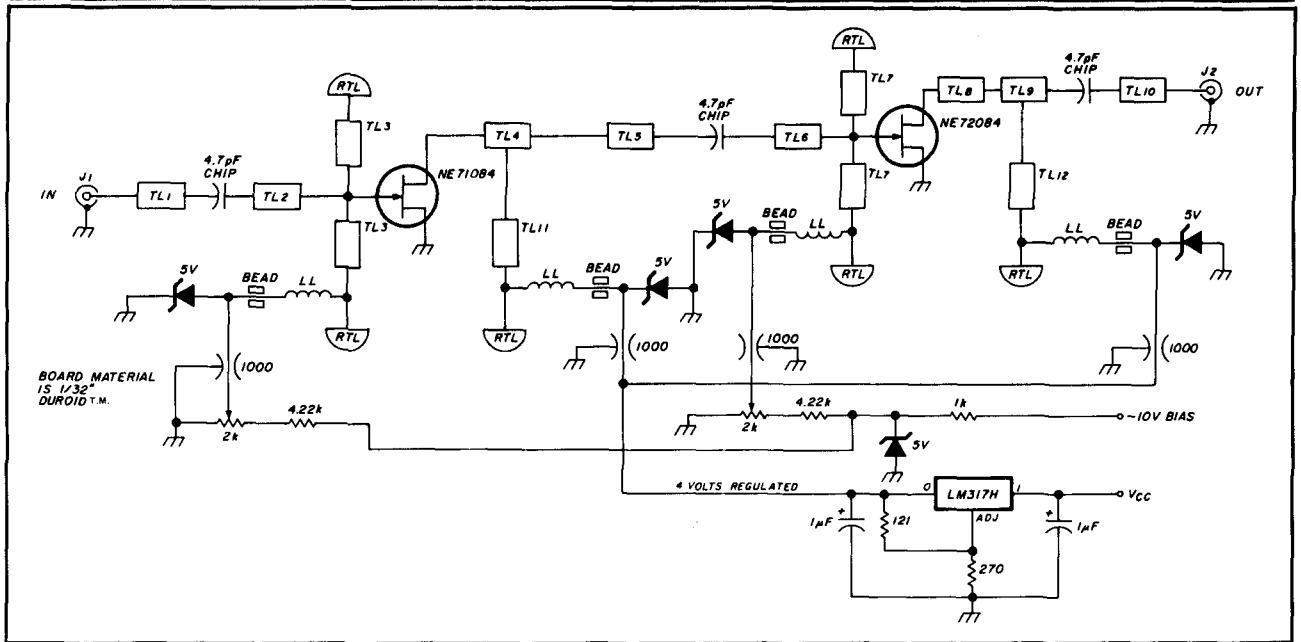
Construction

Unless suitable microwave test equipment is available, you should construct this amplifier after a stable narrowband 10368-MHz station is on the air. Because it needs to be made carefully, the experience gained in getting the downconverter and signal mixers operational should be useful in completing this amplifier.

The first circuits were made by "cutting and peeling" the microstrip traces from a piece of woven double-clad 1/32" TFE (Teflon™-Fiberglass-Epoxy) board material. Rogers Corporation Duroid™ with random fibers was used for the final version because it's somewhat more uniform than woven board material. The woven board material can have a slightly different dielectric constant and shouldn't be substituted for the Duroid.

Use the highest-quality 4.7-pF coupling capacitors, especially in the input stage. About 0.5-dB improvement in noise figure was obtained by changing to high-Q capacitors from run-of-the-mill ones.

FIGURE 9



The two-stage 10-GHz amplifier uses a low noise NE710 in the input stage followed by a less expensive NE720 in the second stage.

Repeatable performance depends upon carefully controlled grounding and component mounting. This is particularly true relative to the transistors themselves. The transistor source leads are soldered to the circuit side ground trace, but front-to-back shorting wires right at the transistor package and plated-through grounding holes are present every 0.100" to maintain good grounding. Careful drilling and wire front-to-back connections should work if a plate-through pc board process isn't available. The "half-moon" radial transmission lines provide an easy way to match impedances and connect bias at the same time. The bias wire can be a resistor lead or small wire soldered right at the junction of the transmission line and the radial line. I put a ferrite bead, held in place by some silicone rubber, on each of these leads for insurance against lower frequency oscillations. The other end of these bias leads connects to its associated feedthrough capacitor. Position the beads away from the circuit board and near the feedthrough capacitors. A 5-volt zener is also connected to each of these capacitors inside the compartment for static and over-voltage protection.

Figure 9 shows the circuit diagram for the amplifier and bias supply. The bias supply (designed by Bob Dildine, W6SFH), provided negative gate bias for this amplifier and higher power transmit amplifiers during the 1987 10-GHz DX record attempts. The LM-10 allows good regulation without needing excess voltage and current to turn a zener diode on hard. Build this supply in a separate shielded enclosure. Use good

quality bypass capacitors on the input and output lines to make sure no switching frequency signals get out and contaminate the rest of the station electronics.

The SMA connectors flanges are soldered right to the board material on both top and ground plane sides. The notch in the board lets the face of the connector flange be flush with the edge of the board. The package is made from 0.030" copper sheeting cut to size, drilled for the feedthrough capacitors or connectors, and then soldered directly to the board as end and side walls. The package adds rigidity to the relatively flexible board material. Flexing can cause excessive strain and coupling capacitor breakage. Therefore, connector solder joints must be kept to a minimum. The SMA connectors are also soldered to the endwalls. Ground the gate and drain the circuits of both devices until you complete the assembly. Carefully assemble the transistors and coupling capacitors on the board with a microscope. Don't use a lot of solder. Take great care with these components; once they're soldered in place there is little chance of removing and reusing them. Interstage partitions can be made from 0.005-0.010" brass shim stock. Notch them just enough to allow clearance for the transistor package and source leads. Carefully solder them in place after the side walls (with feedthrough capacitors and protection diodes) are on. The partitions should protrude about 0.100" above the sidewalls so that the covers can be soldered on after you complete the tune-up. The covers for the interstage and output should have 20-40 ferrite beads glued to their undersides. This suppresses package

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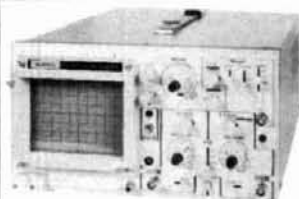
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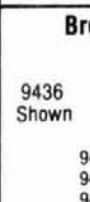
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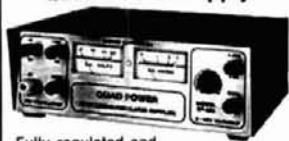


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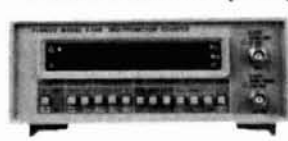


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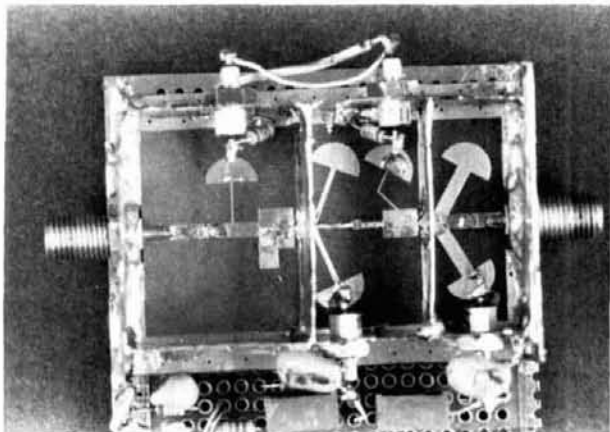
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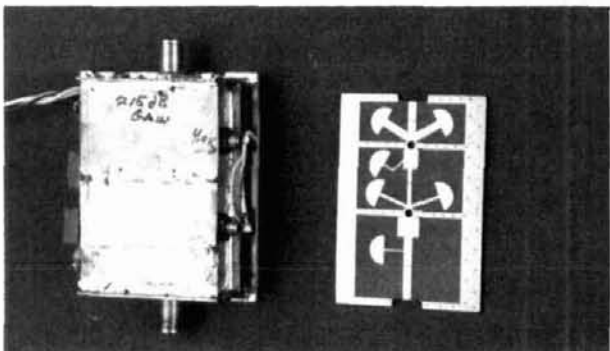
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PHOTO C



The three compartments inside a completed amplifier are visible in this photograph. A shim "tuner" can be seen in the output stage (the largest compartment).

PHOTO D



This photograph shows the amplifier before and after the addition of the copper walls, connectors, and covers. Notches for the connector flanges and holes for the transistor packages are visible on the raw board.

resonances which could degrade performance. The input compartment doesn't have these "absorbers" because any additional losses can degrade noise figure. Crazy Glue™ or similar contact adhesives seem to work and stand the temperature when the covers are finally soldered in place. Photos C and D show the completed amplifier with covers removed.

Tune-up

You can do your tune up once the amplifier and bias circuits are completed, and either a station or other microwave test equipment is available. With the gate bias pots turned all the way down for zero-volts bias, gradually increase the drain supply voltage while watching the drain current. No more than 4.5-volts maximum should be necessary; going much beyond this will cause the protection zeners to start conducting. This zero-bias drain current, IDSS, varies from device to device; note the value for both stages. Next, slowly turn the bias pots to make the gates more nega-

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Output Impedance—50 OHMS Nominal

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FIGURE 10

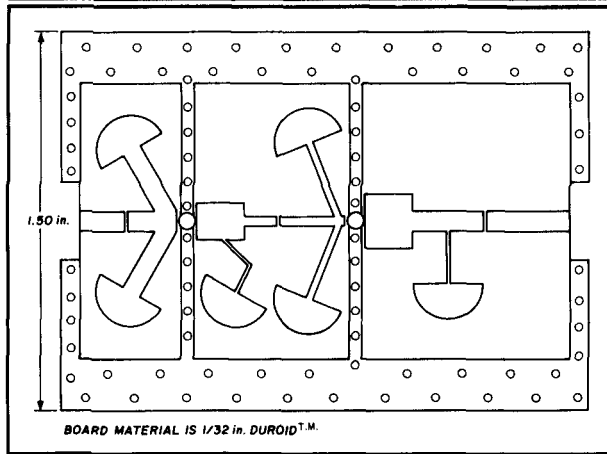


fig. 10A. The original pc board layout for the 10-GHz amplifier.

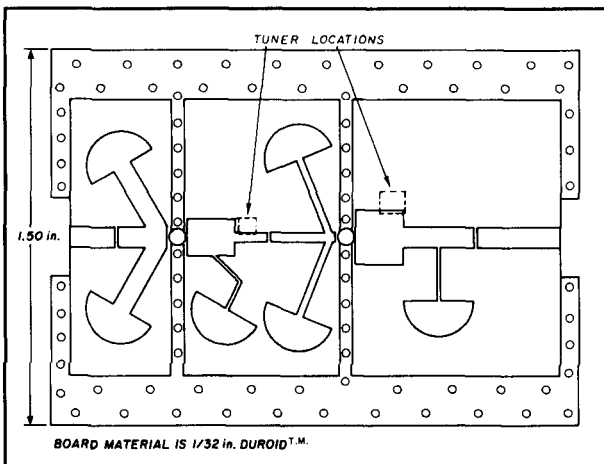
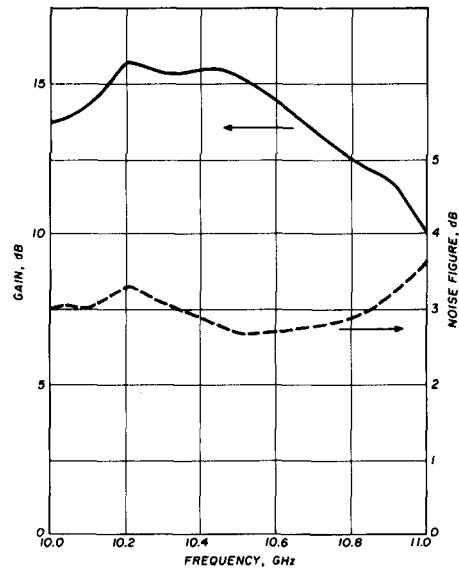


fig. 10B. The pc board layout showing approximate placement of the tuning shims. Note: The shims are glued to the board after finding the exact placement.

tive. The drain current should diminish as you do this. Set the 710-bias current to approximately 25 percent of its IDSS value and the 720 to about 50 percent. You can adjust these later for minimum system noise figure if you have access to measuring equipment, but you should be able to obtain near optimum performance with these settings.

An amplifier like this would require no tuning at lower frequencies. However, a little "tweaking" is useful at 10-GHz, as small variations in construction technique can affect performance. The need to adjust grew out of a mistake in the original design — that of not considering the extra circuit length provided by the gap over which the coupling capacitors are soldered. As a result of this error, untuned gain is about 13 dB. However, by adding small 0.05-0.100" square, 0.002" thick, brass shim stock tuners in the drain-matching circuits of the two stages, the amplifiers can be tuned for maximum gain. This also allows for small device-to-device variations in the transistors. Figures 10A and

FIGURE 11



LL Resistor Lead

TL1 .083"W x .180"L	TL8 .220"W x .188"L
TL2 .083"W x .150"L	TL9 .083"W x .280"L
TL3 .078"W x .277"L	TL10 .083"W x .350"L
TL4 .15"W x .192"L	TL11 .01"W x .250"L (Can be .210"L)
TL5 .039"W x .134"L	TL12 .01"W x .210"L
TL6 .039"W x .220"L	RTL .145" Radius half-circle
TL7 .029"W x .316"L	J1,2 Flanged SMA connector

The measured gain and noise figure of a typical amplifier. More than 15-dB gain and under 3-dB noise figure is readily available.

B show approximate positions for the tuning shims. Tune by first gluing one of the shim tuners at right angles to the end of a toothpick. Carefully use the toothpick to move the shim around, varying the amount it extends past the edge of the transmission line, as well as its location along the length of the line. While you do this, monitor a stable signal on 10368 MHz with the station-receiver S meter. Be sure to maintain contact with the drain-circuit line of the stage. Note the optimum position, turn the power off, ground all bias pins to the amplifier, and permanently solder an identical shim in the position noted. You don't need to perform input-stage tuning because the match provided is not far off, even with the capacitor-gap error. As you can see in fig. 11, minimum noise figure occurs slightly above the hamband calling frequency — but the difference is negligible.

The finished amplifier should exhibit less than 3-dB noise figure and at least 15-dB of gain. On transmit it should be able to deliver 30 milliwatts of linear power and about 50 milliwatts saturated. You may need to increase drain current to more than 50 percent of the IDSS value for maximum output.

Summary

Once the 3456-MHz and 5760-MHz local oscillators are completed, further station improvements will come in the form of better receiver preamps and more transmit power for all the bands. I anticipate that the rapid bandswitch and good system modularity will provide a good contest station, as well as one which can grow with available technology. If you want to build a similar station and try for an obscure record, QSOs on 16-18 different Amateur bands in 2-3 minutes should be possible with this equipment when augmented by a longwire antenna for the hf bands and standard VHF/UHF contest equipment. Another way to use this approach is for 900-MHz band operation. Use a 620-MHz VCO downconverted to a 20-MHz PLL i-f, with an anti-parallel diode mixer like the one used at 1010 MHz. This would give 900-910 MHz operation with the 280-290 MHz i-f.

I have ignored a couple of station components in this series. Transmit/receive switches are necessary in any station using signal frequency amplifiers. Many good units show up at flea markets and surplus stores. I also haven't provided construction information for a good ovenized frequency standard. Although the design presented here showed a 10-MHz standard, a good proportional oven around the unlocked 100-MHz oscillator may provide satisfactory results.

Thanks to Bob Dildine, W6SFH and Lynn Rhymes, WB7ABP for their interest, ideas, suggestions, and help with the station.

Some sources of microwave parts and information.

NEC transistors:

California Eastern Laboratories
3260 Jay Street
Santa Clara, California 95054
(408) 988-3500

Transistors, chip capacitors, mixers, PIN diodes, etc.:

Microwave Components of Michigan
11216 Cape Cod
Taylor, Michigan 48180
(313) 753-4581

An inexpensive (about \$7) surplus 2-8 GHz double-balanced mixer (WJ-M62H) is available from:

HSC Electronic Supply
6819 Redwood Drive
Cotati, California 94928
(707) 792-2277

Article B

HAM RADIO

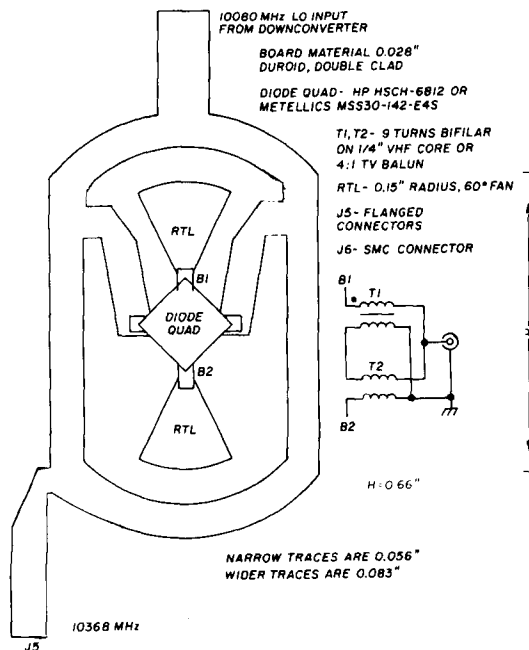
short circuit

Part 2 of "Designing a Station for the Microwave Bands" in the June 1988 edition of *HAM RADIO* needs to be corrected at follows:

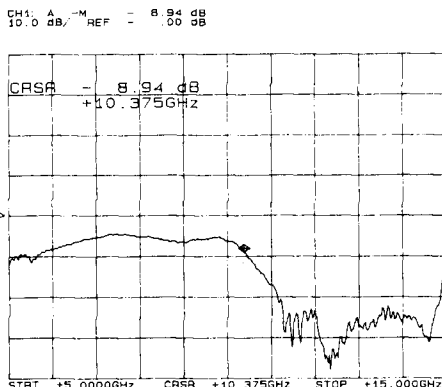
The schematic in fig. 1 on page 20 incorrectly shows

a connection between the 9-volt zener and the 7-nH inductor on the base of Q3. The drawing in fig. 2 shows this correctly.

Although the schematic of the 10-GHz signal mixer in fig. 11 is correct, the implementation shown in figs. 9, 10, and 19 have an error in the positions of the signal and the diode quad connections to the ring. Construction using the dimensions shown results in unnecessarily high conversion loss in the mixer at 10.4 GHz. A corrected fig. 19 is shown here.



Sticky copper tape can be used to correct these errors if you've already made a board to the specifications of the original description. I apologize for any needless effort this may have caused.



As you can see from the plot of conversion loss versus frequency, this mixer is usable but not optimum on both the 5760 and 10368-MHz Amateur bands. Details of a version which is more optimum for 10368 MHz alone is available from the author for an SASE.

Ed.



THE WEEKENDER

REMOTE TUNER FOR 75 METER MOBILES

By Joel Eschmann, K9MLD, 6964 Meadowdale Drive, Hartford, Wisconsin 53027

This article is dedicated to those 75-meter mobile operators who are tired of getting out of their cars to retune their mobile whips every time they change frequency more than 25 kHz!

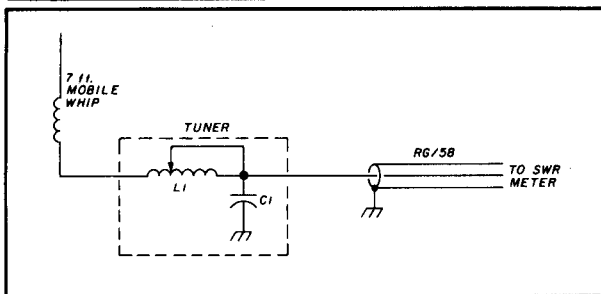
I'm an avid mobile operator on all the hf bands and I have no problem with the bandwidth of my antennas on 20/15/10 meters. But when it comes to 40 and 80 meters, I get frustrated hopping in and out of my car to tune my mobile whip when I QSY. No more! Here's a breakthrough that's so cheap and simple you'll want to use this tuner everywhere, as I have.

It occurred to me that I might use my existing mobile antenna tuned to 4 MHz and add inductance at the base to allow tuning lower in frequency. I wanted to do this across the whole phone band without leaving the front seat of my car.

The schematic in fig. 1 shows that this is a very basic tuner concept found in all the text books. It was a problem finding an inexpensive motor-driven tuner that provided the correct inductance. While looking through many surplus catalogs, I came across a motor-driven Ribbon Roller Inductor at Fair Radio in Lima, Ohio. This silver-plated inductor turned out to be an excellent choice. Its gear train drives a rotary switch that can be used as a limit switch to stop the motor when the inductor gets to the end of its travel.

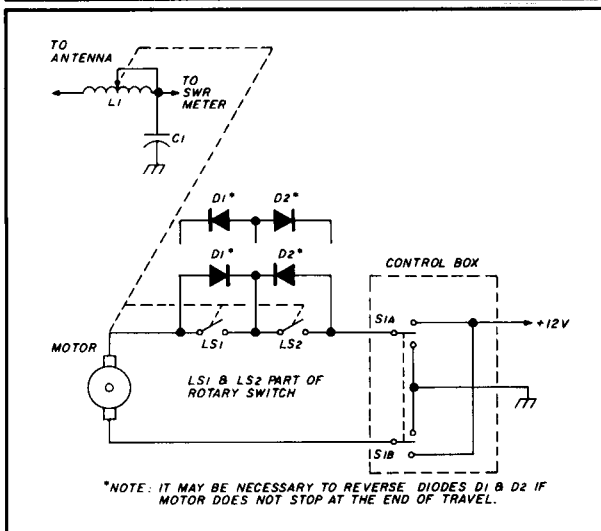
Use the steps that follow to modify the surplus assembly. Remove the top section of the rotary switch; you won't need it. Remove all the wiring from

FIGURE 1



Schematic diagram of the 75-meter remote tuner.

FIGURE 2



Detailed schematic of the limit switch for the roller-inductor drive motor.

parts list

D1, D2 = 1N4003
 C1 = 1000 to 1200 pF mica depending on band of coverage on 80 meters.
 = 500 to 600 pF mica for 40-meter coverage.
 S1 = DPDT switch center off
 Motor Driven Roller Inductor, part no. L401/180L is available from Fair Radio Sales Co., P.O. Box 1105/1106 E. Eureka Street, Lima, Ohio 45802. The price is \$29.95.

the remaining switch section and the motor. A large resistor is mounted on the motor support. This, too, is unnecessary and should be removed. The motor with the resistor in series was designed to run on 24 volts; by removing the resistor you can use it on 12 volts. If you find that the tuner adjustment is too fast, reinstall the resistor and it will slow the tuner down. Reassemble the remaining switch section with the original hardware and rewire it by adding two steering diodes (D1 and D2), as illustrated in fig. 2. It may be necessary to reverse the diodes if the motor doesn't stop at the end of travel.

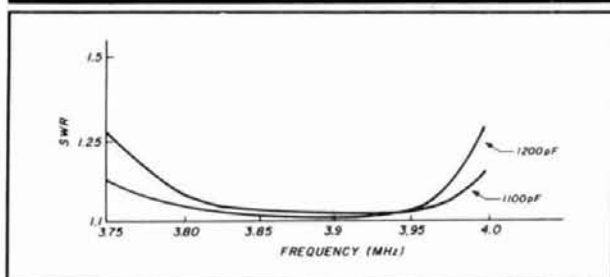
I mounted the motor control box on top of my radio console and used a DPDT center off switch to control the motor. You should mark the control box to

indicate the direction of rotation (which raises the frequency of resonance and which lowers it). Then, taking 12 volts from the ignition switch and routing it to the box, I ran a two-conductor cable back to the tuner at the rear of my car.

A 20-gauge two-conductor cable is all you need to control the motor, as it draws only about 0.2 to 0.3A. Those of you who have automatic tuners in your rigs have probably found that they are quite limited in the amount of SWR they can handle; for those of you who don't, this one will solve all your problems. I have used three of these tuners in my car, my camper, and at home at the base of my 35-foot vertical for tuning 40 and 80 meters.

The tuner tucks away nicely in the rear of my car. I have used this unit successfully in two automobiles with no additional changes. If you wish to operate on 40 meters, just change the shunt capacitance at the input to the tuner. Select this capacitor so you can tune the entire phone band with the appropriate inductance. On 80 meters I used an 1100-pF mica cap; on 40 you'll want to start with about a 500-pF mica cap. Remember to tune your antenna at the top end of the band with no inductance added, then increase the

FIGURE 3



VSWR response curves for the two capacitor values indicated.

inductance as you tune lower in frequency. On 80 meters I was able to indicate a minimum SWR of 1.2 to 1 at 4 MHz and 1.1 to 1 across the band until I got to 3.8, where it started to rise again to 1.2 to 1. Increase the shunt capacitance to 1200 pF to shift the curve lower; change the cap to 1000 pF to raise the curve (see fig. 3).

The last time I talked with Fair Radio there were plenty of these tuners in stock. Let me know if you have any questions and/or enjoy this little tuner. '73 for now and happy mobilizing.

Article C

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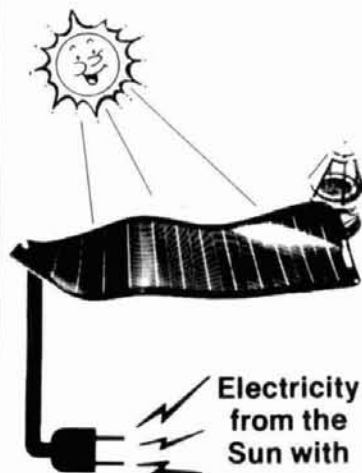
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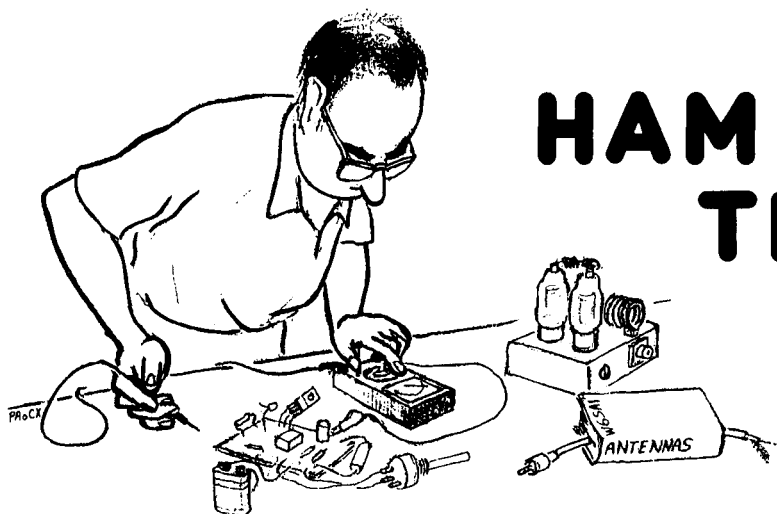
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Bill Orr, W6SAI

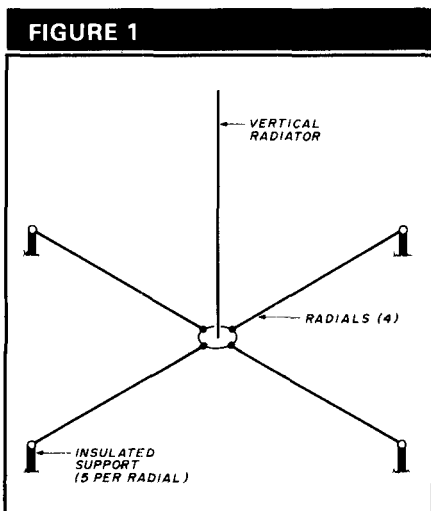


A look at the ground-plane antenna

In April I discussed "Vertical Monopoles With Elevated Radials" by Christman, Radcliff, Adler, Breakall, and Resnick.¹ Their work summarized computer studies indicating that a vertical monopole antenna with four elevated horizontal radials produces more groundwave (low angle) field strength than a conventional ground-mounted monopole with 120 buried radials. The monopole and radials were all a quarter wavelength long and the frequency of operation was 1.0 MHz. Base heights between 5 and 20 meters were investigated. Three different ground constants were used simulating average, very good, and very bad soil conductivity. For average soil, a radial height of 6 meters provided superior performance; for poor soil, a height of 8 meters was required.

The study concluded that "the use of elevated radials would provide superior performance, allowing the collection of electromagnetic energy in the form of displacement currents rather than forcing it to flow through lossy earth in the form of conduction currents."

Figure 1 shows the physical configuration of this antenna design. My remarks on the subject brought letters from readers asking for more informa-



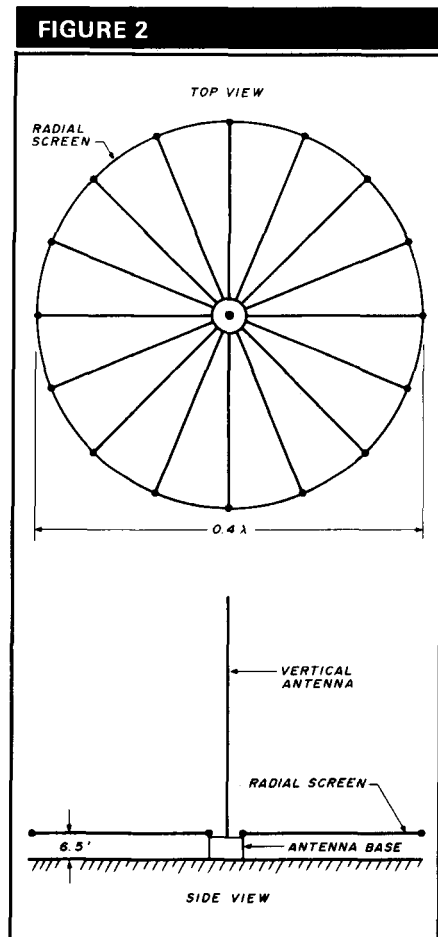
Layout of elevated radial system. Radial height is 6-8 meters at operating frequency of 1 MHz.

tion. There seems to be a great deal of interest in 160-meter vertical antennas.

The concept of above-ground radial wires has been around for a long time. Experiments conducted by Doty, Frey, and Mills^{2,3} and outlined in the 1982 bulletin of the Radio Club of America (later written up in the February 1983 issue of *QST* and also in my column), determined that the traditional ground radial system composed of a number of buried or surface wires can be equaled or bettered by using an elevated ground screen about 6.5 feet off the ground. This is shown in fig.

2. Note that this height is much less than that indicated in the layout of fig. 1.

Although the execution of this ground system is slightly different from



The ground radial system of Doty, et al. uses 50 radials, at least 0.2-wavelength long and 6.5 feet above ground.

the design shown in **fig. 1**, the concept seems to be the same. According to Edward Laport, former vice president of RCA and author of *Radio Antenna Engineering*, "All earth currents should enter the ground wires as displacement currents rather than conduction currents."

Enter the ground-plane antenna

The antennas shown in **figs. 1 and 2** are similar to the conventional ground-plane antenna. Then why all the fuss? A closer look at the ground-plane concept may clear the air. An excellent discussion of the ground-plane antenna was given in the "Technical Topics" column by Pat Hawker, G3VA, in the July 1981 issue of *Radio Communication*.

Pat points out that conventional wisdom (the *ARRL Antenna Handbook*, for example) claims that in order to obtain an omnidirectional pattern, the ground plane requires a metal ground disc with a quarter-wavelength radius (**fig. 3A**). The disc can be simulated with at least four straight radials equally spaced around a circle (**fig. 3B**). This implies that, as with buried radials, the more above-ground radials the better. It also suggests that such an antenna cannot be expected to function efficiently with an omnidirectional pattern with only one or two radials.

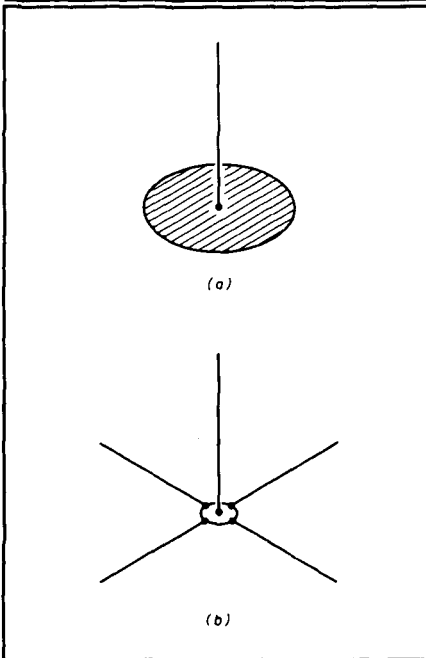
Pat refers to R.C. Hills, G3HRH, who asserts that the radial system of the normal elevated ground plane has little to do with the angle of radiation, but only provides a convenient low potential connection for the shield of the coax line. Hills states that the radials are electrically very transparent and the ground below the radials is well illuminated by the vertical antenna, so the presence of a good ground system is just as important as if the antenna were fed against ground.

G3VA comments on Hills saying, "Here the casual reader would assume that the use of four or more radials plus an extensive earth system buried in ground of good electrical conductivity

was advisable to obtain optimum results."

In summary, G3VA points out that the effectiveness of any vertical antenna in providing low-angle radiation depends to a very marked extent upon earth conductivity. But an earth system that really meets this requirement can't use a normal buried earth system because it should extend many wavelengths around the antenna, in all directions.

FIGURE 3



Solid ground plane having 1/4-wavelength radius (A) can be simulated by four radials, each 1/4-wavelength long (B).

Getting down to basics

The conclusion is that ground conductivity is very important, but this does not answer the puzzle of the number of radials required. As G3HRH pointed out, their prime job is to provide an rf ground point for the coax line and to bring the antenna system to resonance. So why four radials? Why not five? Or three? Or perhaps one?

Pat, G3VA, had the enviable opportunity to meet Dr. George Brown of RCA, the man responsible for the development of the ground-plane antenna. On Dr. Brown's visit to England, Pat put the question to him.

Here's what Pat had to say about this conversation:

"He (Brown) told me that the elevated ground-plane antenna was first devised in the thirties to meet an early requirement for police communications around 30 to 45 MHz. Its success was immediately evident when, at the first demonstration, the transmissions reached well beyond the anticipated service area. Now the important point was that the original design had only two radials; however, when it came to marketing the design the sales engineers reported that they could not persuade potential users that a two-radial antenna, with the two radials looking like a half-wave dipole, could possibly have an omnidirectional radiation pattern. On the classic principle that the customer is always right, George Brown and his colleagues simply added two more radials — and everybody was satisfied."

Pat's conclusion is that all that's required for the ground-plane antenna to function effectively is that the bulk of the horizontal radiation from the radials is cancelled out — and this happens with only two radials. This doesn't prove that four may not be better, but it is an indication that a two-radial ground plane certainly serves the purpose the inventor had in mind!

Separating the two problems

The experiments outlined in **fig. 1** indicate that a radial system is required for a vertical antenna in the vicinity of the earth. They show that a low, but elevated, system of radials is more efficient than a buried system. The data of **fig. 2** point to the same conclusion but indicate that a maximum of only four radials need be used, as opposed to a multiple radial design.

Looking at Dr. Brown's comments with reference to his original design, it is safe to assume that his ground-plane concept envisioned the antenna mounted several wavelengths in the air. The frequency of operation and the need for coverage to the horizon dictated that as great a height as possi-

ble be used. Two radials did the job in this special case. Since the antenna was high above the earth, the return currents entered the radials as displacement currents, and the conduction currents in the earth were quite low because of physical separation of earth and antenna.

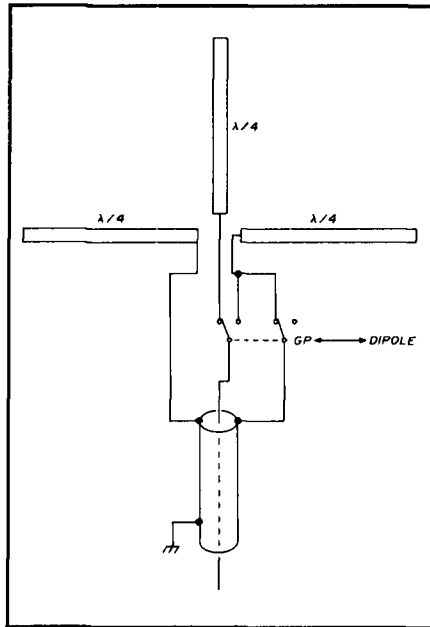
It seems to me that a ground-plane antenna for VHF and hf use, mounted well above the ground, requires but two radials for good omnidirectional performance. On the other hand, when the base of the antenna is mounted close to the ground, the probability of return currents entering the ground as displacement currents is very high.

Dr. Brown's original work on buried ground radials was done in 1936-37. As Arch Doty, K8FCU, says in his article² "Dr. Brown's paper on buried radial wires used with vertical antennas is a true 'classic' work, the excellence of which has established practices in the field ever since. Unfortunately, its very completeness discouraged further research in the area, and the fact that it considered only one of the several possible methods of making artificial ground systems was overlooked."

The Doty, Frey and Mills group and the Christman, Radcliff, Adler, Breakall, and Resnick group have attacked the problem of above-ground radial systems using different methods. The former made physical experiments and conducted ground current measurements using relatively low radials. The latter group employed computer-modeling techniques and investigated field strength using radials at a greater height above ground. Unfortunately, neither group worked with the same radial configuration. Generally speaking, the broad result of both investigative groups was that elevated radials were superior to buried ones.

The first group indicated that 50 elevated radials, at least 0.2 wavelength long and about 6.5 feet above ground, are as effective as 120 buried uninsulated wires. The second group indicated that four radials, about 6 to 8 meters above ground and 0.25

FIGURE 4



Remote double-pole double-throw relay switches from ground plane to dipole antenna.

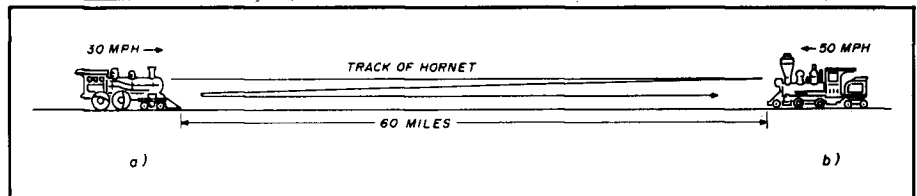
ing scheme like that shown in fig. 4. This will permit the operator to switch from the elevated ground plane (vertical polarization) to a dipole (horizontal polarization) from the operating position. It might provide an answer to the ongoing question: which performs best, a dipole or a ground-plane antenna?

The "Dead Band" Quiz

Here's an age-old problem for the mathematics buff (see fig. 5). Engine A and engine B are on the same track on a collision course. They are 60 miles apart. Engine A is going 30 miles per hour and engine B is going 50 miles per hour.

A fast hornet starts on engine A and flies to engine B, back to engine A, back to engine B, and so on. Eventually the hornet is killed when the two engines collide. The hornet flies at 400 miles per hour. Neglecting the turnaround time of the hornet, wind, and other minor delays, how many miles

FIGURE 5



Engine and hornet problem is this month's quiz.

wavelength long, "produce more groundwave field strength" than 120 buried radials. The first group measured the distribution of ground return currents. The second group examined the radiated field strength by computer. That study indicated that there was very little improvement going from four to 120 above-ground radials.

It remains for future experimenters to study the elevated radial situation. Perhaps a compromise can be found that produces good results with a minimum number of low radials.

A ground-plane dipole combination

The concept of using only two radials for a ground-plane antenna leads to the idea of a remote switch-

does the hornet fly before it's killed in the collision?

Send me your answer to this problem. My address is Box 7508, Menlo Park, California 94025. The calls of the math buffs who provide the most persuasive solution to this puzzle will be given in this column.

References

1. Christman, et al, "Vertical Monopoles With Elevated Ground Systems," Proceedings of the Third Annual Review of Progress in Applied Computational Electromagnetics, Naval Postgraduate School, Monterey, California, March 1987.
2. Arch Doty, "Antenna Efficiency. Is a Ground the Best Ground?" Bulletin, Radio Club of America, November 1982.
3. Doty, Frey, and Mills, "Efficient Ground Systems for Vertical Antennas," QST, February 1983, page 20-25.

Article D

HAM RADIO



HAM PERFECT v 1.0

Action Software has released HAM PERFECT a new MS-DOS program for the Radio Amateur. The program will operate on all MS-DOS computers using DOS 2.1 or later and 256 K of internal RAM. HAM PERFECT is menu driven and includes the following antenna design programs: long wire, vertical, inverted V, tuned transmission lines, electrical length of harmonic wire, and dipole antennas.

A VSWR menu for system evaluation and three DX programs — call area, grid selection, and bearing and distance — is also included. Call area instantly locates any call area, city, or state out of a data base containing 476 records. Displayed are: distance and bearing, sunrise and sunset times, and grid coordinates. Grid selection converts grid to coordinates and vice versa. Bearing and distance gives great circle calculations between any two points on the surface of the earth.

HAM PERFECT sells for \$49.00 and is available from Action Software, P.O. Box 12519, Tucson, Arizona 85718.

Circle #309 on Reader Service Card.

CODEMASTER© Morse code software package

Greenlight Software Development announces CODEMASTER© — their new Morse code software package. The program is IBM compatible and designed for users, from novice to master.

Key features include:

- Menu-driven program for easy selection and use of all facilities.
- One-touch online help function.
- Windowed operating environment for simple maneuvering.
- Escape key for interruption and backtracking.

CODEMASTER© is \$19.95 postpaid and available exclusively from Greenlight Software Development, P.O. Box 2591, Eugene, Oregon 97402.

Circle #310 on Reader Service Card.

New added feature card PK-8 for the CS64S Super Comshack 64

Engineering Consulting's model PK-8 adds new features to the Model CS64S Super Com Shack repeater controller for the C-64. The PK-8 option card makes user-defined talking meters possible. Up to 2 meters per parameter file may be defined (up to 18). Inputs are provided for

talking S-meters, temperature, and battery voltage; any other varying voltages can also be sampled and spoken to the user. The PK8 increases to 16 the total number of external devices which may be activated from your touchtone commands. Two alarm inputs allow real-time Macro commands or may be used to execute alarm messages, whenever these alarm pins are grounded.

The model PK-8 is priced at \$149.95. For more information contact Engineering Consulting, 583 Candlewood Street, Brea, California 92621.

Kantronics KT series and 2.84 firmware option

Kantronics, Inc. has introduced SSB, CW transceivers. There is one each for 80, 40, 20, 15 and 10 meters.

The Kantronics KT series features are noise blanker, 20-watts PEP output, LED digital readout of the entire band in 100 Hertz steps, and receiver incremental tuning (RIT).

Kantronics has also announced a 2.84 firmware option for KAM, KPC-4, KPC-1, KPC-2, and KPC-2400 units:

- Battery Backup for PBBS contents (B.B. "smart socket," and 32K RAM 62256 are extra).
- Protection of PBBS contents during soft reset (changing MAXUsers or NUMnodes will not erase PBBS, battery backup not required).
- Direct keyboard entry of messages into PBBS (limited only by RAM allocation to PBBS).
- PBS subject field (user is prompted for a subject for message).
- Help available from PBBS and KA-Node (gives short description of how to use).
- Enhanced (J)Heard and (N)odes Heard.
- KA-Node recognition of NETROM™ network nodes in its Nodes Heard list.

All Kantronics customers who purchased a Kantronics TNC after March 1, 1988, are entitled to a free 2.84 EPROM. You must provide proof of purchase and request 2.84 when you mail in your warranty card. Be sure to provide the model, firmware level, and RAM part number. If battery backup of RAM is desired, the Battery Backup "Smart Socket" *must be used with a 62256 static RAM!* We strongly suggest using a 32K RAM even if you don't plan to use the battery backup. Both of these are available at extra cost from the factory.

Cost varies from unit to unit, and with the current version level of each.

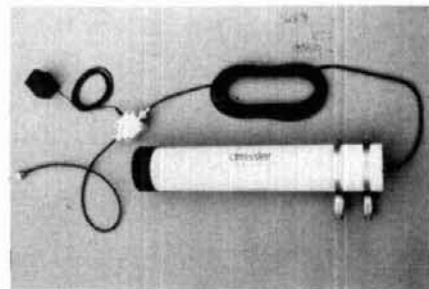
Contact Kantronics, Inc., 1202 E. 23rd Street, Lawrence, Kansas 66046 for details.

Circle #311 on Reader Service Card.

Dressler ara 900 VHF/UHF receiving antenna

The Dressler ara 900 is a VHF/UHF active receiving antenna capable of capturing signals from 50 to 900 MHz. The ara 900 cylinder has an etched circuit board, wideband amplifier, and

impedance-matching network. The antenna's linear characteristics give it excellent intermodulation performance, negative feedback, and a low noise figure. Dimensions are 19-3/4" x 3-5/8" diameter; it can be mounted indoors or



out. The supplied lead-in coax is 25' long and can be replaced by any length coax with PL-259 fittings up to 100'. The coupler terminates in an N-type connector fitting scanners like the Icom R-7000 receiver. Price including power adapter is \$189 plus \$8 shipping and handling. It is distributed by Gilfer Shortwave, 52 Park Avenue, Park Ridge, New Jersey 07656.

Circle #312 on Reader Service Card.

Hamtronics® 900 MHz transmitters

Hamtronics, Inc. has announced a series of transmitters for the 902-928 MHz ham band which complement the R901 FM Receiver.

The new TA901 Exciter runs a minimum of 1/2 watt output, sufficient to run barefoot on short to medium length paths or to drive the new LPA901 Power Amplifier. The TA901 is basically a modified version of the TA451 UHF FM Exciter but a doubler, driver, output stage line-up using surface mount microwave transistors and capacitors replace the usual predriver, driver, and output stages.

The LPA901 Power Amplifier uses a standard heatsink (as on the LPA 2-15 Power Amplifier for the vhf bands) and a broadband power module, which requires no tuning, to produce 8 to 10 watts output. It requires only 100 mW to drive from the exciter.

The TA901 Exciter and LPA901 Power Amplifier are both available off the shelf at \$269 each, wired and tested. (Because of their complexity, these units will not be offered in kit form.) A 902-MHz version of the popular Hamtronics® REP-100 Repeater is also available.

For more information on 900-MHz transmitters, contact Hamtronics, Inc., 65 Moul Road, Hilton, New York 14468-9535. A catalog of other fm transmitters, receivers, repeaters, converters, and preamps for vhf and uhf is available. Send \$1.00 to cover postage or \$2.00 for overseas mailing.

(continued on page 42)



(continued from page 41)



New SSB, CW transceivers

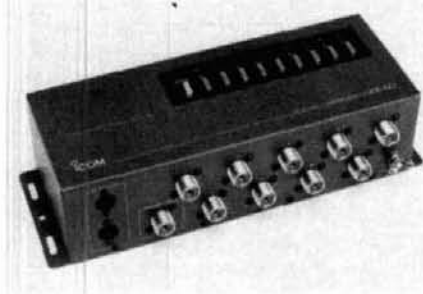
Kantronics, Inc. has introduced five single sideband, CW transceivers. One each for: 80, 40, 20, 15, and 10.

The Kantronics KT series transceiver features 20-watts PEP output, LED digital readout of the entire band in 100-Hz steps and receiver incremental tuning (RIT). Ask your Kantronics Authorized Dealer for information or contact Kantronics, Inc., 1202 E. 23rd Street, Lawrence, Kansas 66046.

Circle #301 on Reader Service Card.

EX-627 hf automatic antenna selector

ICOM now offers the EX-627 HF Automatic Antenna Selector which automatically selects the correct antenna for an ICOM hf transceiver's operating frequency. You can access up to seven antennas by simply pushing one button on the selector.



The EX-627 antenna selector:

- can be used with any transceiver to manually select up to nine antennas,
- includes connectors for a linear amplifier or antenna tuner,
- has power supplied from the transceiver through a provided accessory cable,
- comes with hardware to mount the EX-627 on the wall, the side of a desk, etc.

The suggested retail price for the EX-627 is \$315.00. For more information contact ICOM America, Inc., 2380 116th Avenue, NE/P.O. Box C-90029, Bellevue, Washington 98009-9029.

Circle #303 on Reader Service Card.

Alinco Electronics Inc.

introduces a new line of transceivers, the DJ series hand helds.

Features include:

- Ten memories.
- LCD illumination.
- Dip switch programmable sub-tones. Easily accessible dip switch is mounted on the back of the transceiver.
- Offset storage in memories.
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- Multiple battery packs. 2.5 watts from the factory; 6.5 watts output with optional 12 volt NiCd.



- Sixteen button DTMF pad.
- BNC antenna connection.
- Frequency coverage easily expandable for CAP and MARS.

The suggested list price of the DJ series transceivers is \$299.00.

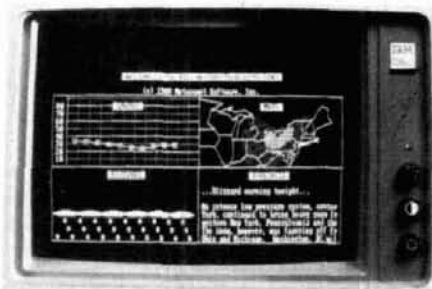
For more information contact Alinco Electronics Inc., 20705 South Western Avenue, Suite 104, Torrance, California 90501.

Circle #302 on Reader Service Card.

Accu-weather forecaster

Metacomet Software in collaboration with Accu-Weather Inc., State College, Pennsylvania, has just announced release of its ACCU-WEATHER FORECASTER software for MS-DOS computers.

ACCU-WEATHER FORECASTER is a menu driven program that allows the user to tap into



Accu-Weather's extensive computerized database. In addition to Accu-Weather's forecasts, you can get hourly updates from National Weather Service Offices nationwide.

Maps, graphs, pictures, charts, and narrative descriptions are just part of what can be downloaded to your MS-DOS computer. To save telephone and hook-up charges, tell your computer exactly what information you want. Then call ACCU-WEATHER; the computer will download the files you want and save them to disk. Information can be obtained for the entire United States or a specific geographical region.

Several different services are available from ACCU-WEATHER. Price varies with the service and time of day that the computer is accessed.

The IBM and Macintosh versions sell for \$89.95. ACCU-WEATHER is available from Metacomet Software, P.O. Box 31337, Hartford, Connecticut 06103 or the ham radio Bookstore. Add \$3.50 for shipping and handling.

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144/220-MHz FM dual bander

Kenwood's all new 144/220-MHz FM Dual Bander TM-621A includes a dual channel watch function, selectable full duplex operation, 30 memory channels, extended frequency coverage, large multi-color dual digital LCD displays, and programmable scanning, with 45 watts of output on 144 MHz and 25 watts on 220 MHz.

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- Automatic offset selection on both bands.
- Dual frequency display for "main" and "sub-band."
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(continued on page 102)

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by Alberta Wallen

Born at the very beginning of the radio age, Harold Beverage is one of radio's pioneers. Most know him from his development of the Beverage or wave type receiving antenna. Learn about the career of this brilliant engineer in this easy-to-read biography. Starting with GE in 1917 and moving to RCA in 1920, Beverage was involved in some of the most exciting aspects of radio. Of particular interest is a reprint of the famous November 1922 QST article describing the wave antenna. Includes 35 photos. 130 pages ©1988

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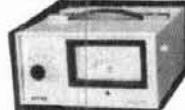
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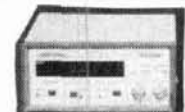
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PATHFINDER

PART TWO

By Ron Todd, K3FR, 7 Hillcrest Road, Windham, Maine 04062

Add output option menu
and file access functions
for complete operating aid

When I originally defined PATHFINDER¹ I wanted a program that would bring together three major utilities regularly used to map hf operating activities: MINIMUF², bearing/distance, and grey-line summary. Part 1 showed how these three seemingly different functions all rely on the same basic set of mathematical routines, and presented the core program of PATHFINDER. If you've read part 1, you know that PATHFINDER is a menu-driven program that reports bearing and distance, home and target terminator events, MUF for short and long path to the target specified, and the radial MUF for a given time and path length. Conditions may be changed and analysis selected at will to provide a general view of propagation modes and conditions. However, PATHFINDER is cumbersome to use because coordinates must be entered manually.

The *ARRL Antenna Handbook* is a handy reference for your target coordinates.³ At the back of the book is a listing of DXCC countries with their geographic coordinates. But, when using a reference table of location coordinates, there's still the chance that you might enter a coordinate incorrectly and waste time rerunning a simulation. There are two other features PATHFINDER might provide once you've established a latitude/longitude data file. These are a global summary report of grey-line conditions from your home location to any location in the data file which has terminator concurrency, and a summary listing of bearing and distance from the home QTH to all locations in the data file.

This month I'll give you a program to generate a data file of prefix, location name, and geographic coordinates. I'll also include the appropriate code to insert

into PATHFINDER to allow either case specific or global access to this data file. The case specific feature eliminates the need to maintain a desk reference when using PATHFINDER in a point-to-point mode. Global access lets PATHFINDER generate the world bearing and distance report, or report all QTHs on or near your grey line. I've added an expanded hard copy function which is accessed through a second menu level when you want printer output. The menu provides selection of either a chart or tabular format report of the latest MUF run, or a listing of the current conditions and locations defined.

Getting more out of PATHFINDER

The charting feature of the expanded hard copy function is, like the current list feature, built around the array MOUT which is loaded during each analysis run. The current list option of the top level menu sent the data in this array to your printer. The charting option does the same, but presents the MUF data in a simple graphic form by tabbing your printer to a specific column. In the MOUT (36) array the index is equivalent to the independent variable of the analysis, while the array content is the analysis result for each increment of the independent variable. Choose the hard copy report function after each MUF run to get your report. The tabular report is still presented on screen as the analysis is running, so you can choose to output the report or run further analyses until you have one you want to keep.

Those of you using the hard copy function have noted that the conditions under which the MUF is reported aren't listed to the printer. A third option is added to the new hard copy second level menu to allow printout of this information. With only the output enhancements added, the new top level menu looks like:

Opt: 1 = Input 2 = Anal 3 = Output 4 = Quit

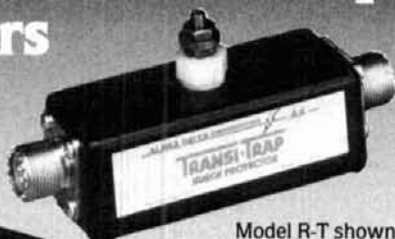
and the output function select menu shows the selections available:

Opt: 0 = Top 1 = Table 2 = Chart 3 = Data

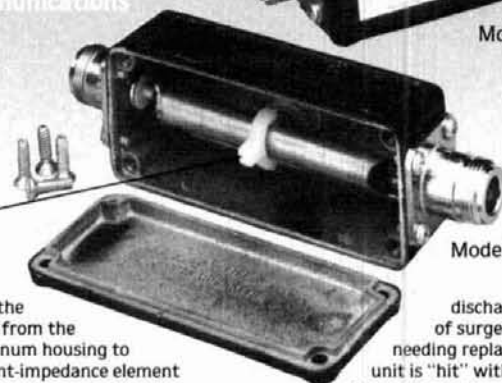
Figure 1 gives the steps and lines required to add these features to your copy of PATHFINDER, along with

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FIGURE 1

```

Modifications to PATHFINDER to add chart and data output to
line printer routines.

Replace line 200 with:
200 INPUT "Opt: 1-Input 2-Anal 3-Output 4-Quit ";IO

Replace lines 290 thru 320 with:
290 INPUT "Opt: 0-Top 1-Table 2-Chart 3-Data";IO
300 ON IO GOSUB 310,350,390: GOTO 200
310 LPRINT "GMT/DEG","MUF","GMT/DEG","MUF"
320 FOR IH=0 TO I-1: FOR IB=0 TO I STEP 1

Add new lines 330 thru 450.
330 LPRINT (IH+IB)*IA,MOUT(IH+IB),
340 NEXT IB: LPRINT: NEXT IH: RETURN
350 FOR IH=0 TO 2*I-1
360 LPRINT (IH*IA);TAB(6+INT(MOUT(IH)));"": NEXT IH
370 LPRINT " | 10 | 20 | 30 | 40 | 50"
380 LPRINT: RETURN
390 LPRINT "Path length =";INT(G1*3959);"miles"
400 LPRINT "Path bearing at home OTH =";INT(PB*PI)
410 LPRINT "DATE: "MID$MS,3+MO-2,3) " DG
420 LPRINT "HOME AT LAT"LT"LONG"WH" TARGET AT LAT"LT"LONG"MT
430 LPRINT "SOLAR FLUX="SX" SUN SPOT NUMBER="S9
440 IF IL=2 THEN LPRINT "TIME: ";INT(40+INT(T5)+60*T5)/100;"Z"
450 RETURN

```

Modifications to PATHFINDER to add chart and data output to line printer routines.

the changes and additions needed to add the expanded hard copy functions to the program. The scope and nature of these changes have been limited to add, delete, and replace functions. If you use a word processor, note that some of these and the later changes amount to no more than renumbering and moving some lines so that they occur in a revised sequence. This can save you some time in implementing these enhancements. If you don't use your word processor for this task, input new lines to your BASIC rather than using its RENUM command. The RENUM command will renumber all lines beyond the first target number and cause all sorts of headaches when you implement the rest of the features.

At this point you can choose either a tabular or a chart format printer listing of MUF. You can also obtain a list of the current input data so that you won't have to annotate your listings in order to remember what the output is telling you. I assume you all have fat fingers like me and would benefit from some debugging; it would be a good idea to practice the new PATHFINDER features before continuing on to the data file access features.

Blazing speed

The grey-line daylight characterization routine in PATHFINDER wasn't optimized in the original version. This makes little difference when you're doing individual specific grey-line evaluations, but will slow down the grey-line summary when it's added. Figure 2 shows modifications that create a separate subroutine to compute the solar events and merge this routine into the one needed to determine the solar driven parameters for MUF computations. Again, the changes may be done with your word processor working on an ASCII version of the program.

Data makes THE difference

PATHFINDER's prime limitation in its original form

FIGURE 2

```

Modifications to PATHFINDER to accelerate GREY-LINE computations
Change lines 1300 and 1310 to:
1300 W0=W1: L0=L1: GOSUB 5100: PRINT "At home QTH": GOSUB 7000
1310 GOSUB 8420: W0=W2: L0=L2: GOSUB 5100: PRINT "At targ QTH"

Replace lines 5000 thru 5040 with:
5000 GOSUB 5100: IF C0(I)<=86 THEN 5040 'SOLAR CHAR
5010 IF C0(I)<=2004 THEN T9(I)=1: ELSE T9(I)=9.7*C0(I)^.6
5020 X=R9(I)/T9(I): SW(I)=PI/X: G8(I)=C0A/(1+SW(I)^2): GOSUB 6100
5030 X(I)=(EXP(-X)+1)*SW(I)+G8(I): G7(I)=EXP((R9(I)-24)/2)*SB(I)
5040 RETURN

Delete lines 5050 thru 5090.

Replace lines 5100 and 5110 lines with:
5100 R9(I)=0: X=10*X2: C0(I)=COS(X): C0A=COS(6*X/7) 'DAY CHAR
5110 IF C0(I)<=86 THEN 5170 ELSE R8=6*(2+W0*P2)-BT 'DAY CR

Add new lines 5120 thru 5170:
5120 IF R8<0 THEN R8=R8+24 ELSE IF R8>24 THEN R8=R8-24 'MOON
5130 BS=COS(V2)*COS(L0): IF X<.0001 THEN X=.0001
5140 X=(SIN(V2)+SIN(L0)-86)/X: GOSUB 6000: X=6*X*P2: K9(I)=2*X
5150 BR(I)=R8-X: IF BR(I)<0 THEN BR(I)=BR(I)+24 'SUNR
5160 SB(I)=R8*X: IF SB(I)>24 THEN SB(I)=SB(I)-24 'SUNB
5170 RETURN

```

Modifications to PATHFINDER to accelerate GREY-LINE computations.

FIGURE 3

```

Program to create or edit a sequential data file.
10 DEFINT I: 'PROGRAM GENDAT.BAS, RCT 4/11/88
20 INPUT "4-Delete 5-New 6-EXIT":IO
30 ON IO GOTO 10,200,300,400,500,1000: GOTO 20
100 GOSUB 700: IF NOT EOF(1) THEN PYS="": GOSUB 800 'ADD TO END
110 GOSUB 600: BS="": INPUT "<CR> to Continue, else Done";B5
120 IF LEN(B5)=0 THEN 110 ELSE 750
200 GOSUB 700: IF EOF(1) THEN 760 'EDIT RECORD
210 INPUT "EDIT PREFIX: ";PYS: GOSUB 900: IF EOF(1) THEN 760
400 GOSUB 700: IF EOF(1) THEN 760
220 GOSUB 600: BS="": INPUT "<CR> to Continue, else Done";B5
230 IF LEN(B5)=0 THEN 210 ELSE 750
300 GOSUB 700: IF EOF(1) THEN 760 'INSERT RECORD
310 INPUT "ADD AFTER PREFIX: ";PYS: GOSUB 900: IF EOF(1) THEN 760
320 WRITE #2,PXS,Q5,L2,W2
330 GOSUB 600: BS="": INPUT "<CR> to Continue, else Done";B5
340 IF LEN(B5)=0 THEN 330 ELSE 750
400 GOSUB 700: IF EOF(1) THEN 760 'DELETE RECORD
410 INPUT "DELETE PREFIX: ";PYS: GOSUB 900: IF EOF(1) THEN 760
420 BS="": INPUT "D to Delete, else Reject";B5
430 IF NOT (BS="D" OR BS="d") THEN WRITE #2,PXS,Q5,L2,W2
440 BS="": INPUT "<CR> to Continue, else Done";B5
450 IF LEN(B5)=0 THEN 410 ELSE 750
500 OPEN "O",#1,"LATLONG.DAT": CLOSE #1: GOTO 20 'CREATE NEW FILE
600 INPUT "File#,PXS: INPUT "QTH";Q5 'CAPTURE DATA
610 INPUT "Latitude ";L2: INPUT "Longitude ";W2
620 PRINT ".... PLEASE CHECK DATA ...."
630 BS="": INPUT "<CR> IF OK, R to Redo, else QUIT";B5
640 IF LEN(B5)=0 THEN WRITE #2,PXS,Q5,L2,W2: RETURN
650 IF (BS="R" OR BS="r") THEN 600 ELSE RETURN
700 OPEN "I",#1,"LATLONG.DAT" 'OPEN FILES
710 OPEN "O",#2,"TRAP.DAT": RETURN
750 PYS="": GOSUB 800 'COPY REST OF FILE AND CLOSE ALL
760 PRINT "END OF FILE": CLOSE #1: CLOSE #2: KILL "LATLONG.DAT"
770 NAME "TRAP.DAT" AS "LATLONG.DAT": GOTO 20
800 IF NOT EOF(1) THEN INPUT #1,PXS,Q5,L2,W2 ELSE RETURN 'REARCH
810 IF PXS<PYS THEN WRITE #2,PXS,Q5,L1,W2: GOTO 800 ELSE RETURN
900 GOSUB 800: IF EOF(1) THEN RETURN 'FIND RECORD
920 PRINT "Found: ";PXS;" Q5:";L2;" Lon=";W2
930 BS="": INPUT "<CR> IF OK, N for NEXT, else to QUIT";B5
940 IF LEN(B5)<0 THEN WRITE #2,PXS,Q5,L2,W2 ELSE RETURN
950 IF NOT (BS="N" OR BS="n") THEN PYS="":
960 GOTO 900
1000 BS="": I=0 'MAKE KEY FILE, EXIT
1010 OPEN "I",#1,"LATLONG.DAT": OPEN "O",#2,"LATLONG.KEY"
1020 IF EOF(1) THEN 1090 ELSE I=I+1: INPUT #1,PXS,Q5,L2,W2
1030 AS=LEFT$(PXS,I): IF AS=AS THEN 1020 ELSE BS=AS: J=I-1
1040 IF=ASC(BS)-65: IF IP>31 THEN IP=IP-32
1050 IF IP>25 THEN 1020
1060 IF (IP=15) AND (IP<=7) THEN IP=IP+43
1070 IF (IP=0) AND (IP<=36) THEN WRITE #2,IP,J
1080 GOTO 1020
1090 CLOSE #1: CLOSE #2: END

```

Program to create or edit a sequential data file.

was that you had to know the geographic coordinates of the target station. Many serious DXers keep a listing of bearing and distance information on their desks, or use some other operating aid to help point their antennas. Sometimes these indexes include the geographic coordinates at the location of interest; often they do not. Your computer gives you an excellent card box in which to keep this information. Next, I'll tell you how to get this information into PATHFINDER.

Your computer keeps its information in files on tape or disk. When you save program data to one of these

files, the operating system arranges and catalogs the data for you so that you can find it later. Generally there are two types of files used for this information storage: sequential and random. Sequential files can usually hold any type of information in any order, but data must be accessed in the same order as written from beginning to end. Random files can be accessed at will, but may contain only strings (character data) of fixed format. While random files allow quicker access to data stored deep in the file, more complex operations are usually required to get the data into and out of it. Additionally, some dialects of BASIC don't even implement random access files. I'll present only code to generate and access sequential files.

When generating your data file, you can choose from several sources of geographic coordinates to create the locations contained in that file. My own data file was taken from Overbeck and Steffen.⁴ In addition to the ARRL publication mentioned previously, a world atlas (like those published by the Rand McNally Company or Encyclopedia Britannica, Inc.) can provide a source for the data you need. Your local library should have one of these references.

The listing in **fig. 3** is the code for GENDAT.BAS. This program creates and edits a sequential file called LATLONG.DAT that will hold the data PATHFINDER needs to set a target QTH. At the end of the program, GENDAT reads the file just edited and creates a key listing file. This file tells PATHFINDER approximately where in the data file it can find the prefix you enter, based on the first character of that prefix. The program requires that both LATLONG.KEY and LATLONG.DAT be on the default disk. This must be the same disk you are using to run PATHFINDER and BASIC.

GENDAT prompts you for the information it needs to build the data file. At the end of each entry, you'll be asked to verify the information you have supplied before the data is written to disk. Take this step seriously; any error in the data will reflect on PATHFINDER's accuracy.

Select NEW (item 5) at the first menu prompt the first time you run GENDAT. This assures the program that it will find a file when it needs to. After that you can add to the end of the file, edit an entry, insert an entry in the middle, or delete an entry by making the appropriate menu selection and answering the prompts. You needn't finish the job in one session; that's why there are selections for all functions. If you already have a satisfactory LATLONG.DAT file in the specified format, just invoke GENDAT and then select QUIT (item 6) at the first menu prompt. This will generate the key file from your current data file without changing the data file.

You can use a word processor in the program-writing mode instead of GENDAT as long as you enter the data in the order of prefix, QTH name, latitude, and longitude. But you'll have to quote the string fields (prefix and QTH

name), separate each field with a comma, and terminate each line with a carriage return. GENDAT may not be as fast or as flexible as a word processor, but it does order and delimit the data for you. If you do use a word processor, make sure you build a small program to create the key file. The code for this is in lines 1000-1090 of GENDAT.BAS. Without the key file, PATHFINDER will either fail to function or, at the very least, will take more time in finding a QTH for you. If you are a good typist and feel comfortable with your word processor then go ahead and use it; otherwise, I highly recommend that you key in and use GENDAT.

Whichever way you choose to create your data file, the prefix *must* use capitals for *all* its alphabetic characters! Another thing to remember when preparing your data file is that you *must* group all locations according to the first character of the prefix (all G's together, all U's together, all 1's, etc.) Though it's not necessary to arrange these groups alphabetically, it's easier to do so as the searching process will run a little faster and the bearing/distance and grey-line summaries will print out in order. I haven't worked out a simple way to access a country without an assigned prefix (Abu-ail), so you'll have to code it as some strange numeric or alphabetic call; try "ABU" for instance. Do not, however, use an asterisk (*) for these calls; GENDAT uses this character as a default to terminate searches.

The keys to the kingdom

Now that you have data and key files, how does PATHFINDER use this information to set QTHs? In order to minimize the search time on the sequential LATLONG.DAT file, I have implemented a key file called LATLONG.KEY. This file has up to 36 integer pairs which tell PATHFINDER how far into the data file it must read before reaching an entry with the same first character as the prefix you're looking for. The keys are based on an ordinal value assigned to the letters of the alphabet and the numerals (letters from 0-25 and numerals from 26-35). The first integer in the pair is the ordinal value of the first letter/number of the prefix; the second integer is the number of records that must be read before the program can read a record with the same prefix first character.

When you enter a prefix to PATHFINDER's prompt, the program takes the first character in the prefix, determines its ordinal number in the same way GENDAT does, and then looks in the array IKEY for the index number corresponding to this character. Using this index number the program will open the LATLONG.DAT file, read and discard that many locations, and then start checking the prefix of the data file location for a match to the prefix you requested. When the program finds a matching prefix, it displays the location associated with it and checks with you to see if it's the one you want.

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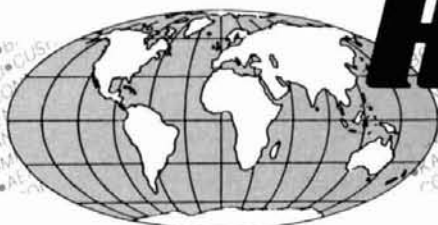
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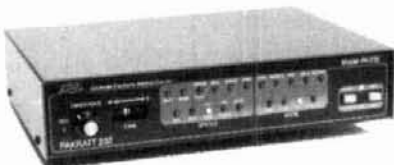
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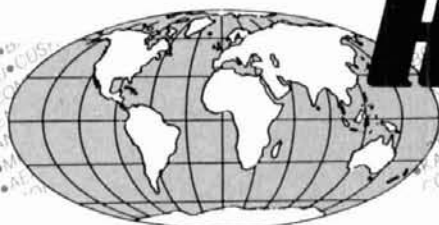
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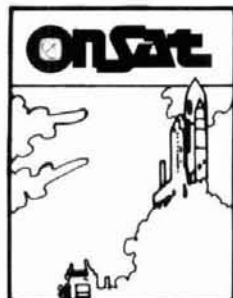
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FIGURE 4

```

Pathfinder modifications to add data file access and summary menus
Replace lines 200 and 210:
200 INPUT "Opt: 1=Input 2=Anal 3=Output 4=File 5=Quit ";IO
210 ON IO GOTO 220,240,280,460,9999: GOTO 200

Add lines 72 thru 78.
72 DIM IKEY(35): OPEN "I",1,"LATLONG.KEY" 'LOAD KEY ARRAY
74 FOR IP=0 TO 35: IKEY(IP)=1: NEXT IP
76 IF NOT EOF(1) THEN INPUT #1,IP,IKEY(IP): GOTO 76
78 CLOSE #1

Add lines 460 and 470.
460 INPUT "Opt: 0=Top 1=B/D 2=Grey 3=Target ";IO
470 ON IO GOSUB 500,600,800: GOTO 200

```

PATHFINDER modifications to add data file access and summary menus.

FIGURE 5

```

PATHFINDER modifications to add data file access functions.
Add lines 500 thru 580, 600 thru 780 and 800 thru 940.
500 OPEN "I",1,"LATLONG.DAT" 'BEARING/DISTANCE LIST
510 LPRINT "PREFIX" TAB(15) "QTH" TAB(48) "SHORT PATH" TAB(68) "LONG PATH"
520 LPRINT TAB(45) "BEARING DISTANCE" TAB(65) "BEARING DISTANCE"
530 IL=0: IF EOF(1) THEN 570 ELSE INPUT #1,PXS,QS,LT,WT
540 LPRINT PXS TAB(10) LEFT$(QS,30); GOSUB 8420
550 GOSUB 3000: I=45: IA=53: GOSUB 580: IL=1
560 GOSUB 3000: I=65: IA=73: GOSUB 580: LPRINT: GOTO 530
570 CLOSE #1: RETURN
580 LPRINT TAB(1) INT(PB*RI) TAB(IA) INT(IG1*3959);: RETURN
600 I=1: IL=0: SD=0: WD=0: LD=2: OPEN "I",1,"LATLONG.DAT" 'GREY LIST
610 GOSUB 5100: IF CO(I)<=86 THEN PRINT "NO SUN AT HOME":GOTO 780
615 LPRINT "Home Sunrise at:";INT(40*INT(SR(I))+60*SR(I))/100;"Z"
620 LPRINT "Home Sunset at:";INT(40*INT(SS(I))+60*SS(I))/100;"Z"
625 LPRINT "PREFIX" TAB(15) "QTH" TAB(48) "AT SR" TAB(63) "AT BS"
630 LR1=SR(I)-.75: LR2=SR(I)+.75: LS1=SS(I)-.75: LS2=SS(I)+.75
640 IF EOF(1) THEN 780 ELSE INPUT #1,PXS,QS,LT,WT: GOSUB 8420
645 LD=L2: WD=W2: GOSUB 5100: IF CO(I)<=86 THEN 640
650 IRR=0: IRS=0: ISR=0: ISS=0: X=SR(I): Y=SS(I)
660 IF LR1<0 THEN IRR=(X-24)>LR1: IRS=((Y-24)>=LR1)
665 IF LR2>24 THEN ISR=(X-24)>=LR2: ISS=((Y-24)>=LR2)
670 IF LR2>24 THEN ISR=(X-24)<=LR2: ISS=((Y-24)<=LR2)
675 IF LS2>24 THEN ISR=(X-24)<=LS2: ISS=((Y+24)<=LS2)
680 IF IRR OR IRS THEN 690
685 IRR=(X>LR1)AND(X<=LR2): IRS=(Y>=LR1)AND(Y<=LR2)
690 IF ISR OR ISS THEN 700
695 ISR=(X>=LR1)AND(X<=LR2): ISS=(Y>=LR1)AND(Y<=LR2)
700 IF (IRR OR IRS OR ISR OR ISS) GOSUB 720
710 GOTO 640
720 LPRINT PXS TAB(10) LEFT$(QS,30) TAB(45);
730 IF IRR THEN X=SR(I): AS="SR": GOSUB 770: GOTO 740
735 IF IRS THEN X=SS(I): AS="SS": GOSUB 770
740 LPRINT TAB(60);
750 IF ISR THEN X=SR(I): AS="SR": GOSUB 770: GOTO 760
755 IF ISS THEN X=SS(I): AS="SS": GOSUB 770
760 LPRINT: RETURN
770 LPRINT INT(40*INT(X)+60*X)/100;"Z ";AS: RETURN
780 CLOSE #1: RETURN
800 INPUT "PREFIX TO SEARCH FOR";PYS 'TARGET FROM FILE
810 IP=ASC(LEFT$(PYS,1))-65: IF IP=31 THEN IP=IP-32
820 IF IP<25 THEN PRINT "ERROR": GOTO 800
830 AS=CHR$(65+IP): IF (IP<=7 AND IP>=18) THEN IP=IP+43
840 IF (IP<0)OR(IP>35) THEN PRINT "ERROR": GOTO 800 ELSE IF=IKEY(IP)
850 OPEN "I",1,"LATLONG.DAT": IF IP<0 THEN 930
860 FOR I=0 TO IP: INPUT #1,PXS,QS,LT,WT: NEXT I: GOTO 890
870 IF EOF(1) THEN 930 ELSE INPUT #1,PXS,QS,LT,WT
880 IF LEFT$(PXS,1)>AS THEN 930
890 IF PXS<>PYS THEN 870 ELSE PRINT "Found: "PXS" in "QS
900 BS="": INPUT "CR" IF OK, N FOR NEXT, else to QUIT: BS
910 IF LEN(BS)=0 THEN LT=LT: WT=WT: GOSUB 8420: GOTO 940
920 IF (BS="N")OR(BS="n") THEN 870
930 PRINT "NOT Found"
940 CLOSE #1: I=1: RETURN

```

PATHFINDER modifications to add data file access functions.

Some prefixes have more than one location associated with them; you may check each one in sequence until you have selected the one you want. PATHFINDER continues this activity until the prefix no longer matches and then closes the file. You can cut this process short by telling the program to terminate the search. When you accept a location, PATHFINDER copies the latitude and longitude to the target location and then returns to the top level menu.

The index array is built once at the beginning of the program execution by reading in the key values from the LATLONG.KEY file. Some prefix first characters (M, Q, etc.) may not occur in the data file. GENDAT doesn't store a data pair for these characters; PATHFINDER

handles this situation by preloading the IKEY array with a default value which is overwritten by those locations which do occur. When you input a nonoccurring prefix PATHFINDER extracts the default value from the array and, knowing that the prefix does not exist, it then exits the search function.

Now add the code for the data file access. Figure 4 details the changes which must be made to the top level menu — the additional lines needed to declare and load the key array and the additional program lines that define and implement the file level menu. These changes are rather simple. The new top level menu looks like:

Opt: 1 = Input 2 = Anal 3 = Output 4 = File 5 = Quit and the file level menu is:

Opt: 0 = Top 1 = B/D 2 = Grey 3 = Target

Note that the QUIT selection in the top level menu changes to 5 to make a sensible space for the file operations.

This is a good time to do some checks. After saving the program, type in lines 500, 600, and 800 with a simple print statement and a return statement to show which target you have accessed. Now run the program and exercise the menu selections. It isn't necessary to save the program here unless you have to make corrections.

Figure 5 gives the code to accomplish the file-based functions. Insert these lines into the big hole of program line numbers preceding the hourly MUF driver at line 1000. The space provided in the original PATHFINDER coding ended up being a little too tight to maintain MODULO 10 line numbering (particularly in the grey-line list section) but, with a little squeezing of line numbers, the code fits. The function of this code is broken down into three main subroutines. Lines 500-570 generate the bearing/distance report summary; line 580 is a subroutine which is called to print the bearing and distance. The code from lines 600-780 does the grey-line summary and calls the subroutine in lines 720-760 to print a line. If the location is on your grey line, this subroutine calls another at line 770 to print the time and condition of the target grey line. The routine to search for a location in the data file is in lines 800-940.

The finished product

You'll have a fairly sophisticated operating aid after making all these modifications to PATHFINDER. Anything comparable costs a lot more than two copies of *HAM RADIO*, and chances are the MUF algorithm isn't as good and doesn't run as fast. PATHFINDER can do a lot for almost any Amateur who has his own hf equipment. I recently discovered one application in the field of antipodal DX.⁵ After entering the date and solar flux, execute a radial MUF projection with a path-length hop value of 5 and any hour you choose. The radial report will show you the MUF for each bearing to your antipode.

Try those bearings which show a MUF near the band you intend to work.

In the global modes PATHFINDER accesses the data file one location at a time and uses these locations as the target for any computation required. The bearing/distance reports are printed for each location while the grey-line summary includes only those locations which have a grey line within 45 minutes of one of your grey lines. Since the grey-line summary already takes a lot of time, there's no suggested MUF for this report. If you're interested in the MUF for a particular grey-line path, run the point-to-point MUF for that location.

You can achieve expanded utility of the file-based features by generating several data files, based on your own operating habits, and queue for a file name to use in generating the summary reports. Your summaries would take less time because they would be accessing fewer locations in your data file. For instance, you could delete all the domestic locations or all the locations that could never have a common terminator from the grey-line file you use.

Another suggestion is to make several data files based on continent or region of the world and select the one which interests you at the time. There is nothing magical about the prefix value in the data files. You might want to enter the state or country name in this field rather than a prefix. These tactics would be particularly beneficial if you use the grey-line summary frequently or want to separate bearing/distance reports for each region. Just remember that you'll have to load the key array corresponding to the data file selected.

Sorts can become complicated and, with the amount of storage a sort might require, I decided to avoid this nicety in PATHFINDER. You are welcome to implement your own to get your grey-line report in a time sequential format. If you wish to convert the data file to a random access file, note that the key array and key file offer an open door to a significant improvement in performance and expanded utility. A revision of the grey-line test ranges is another customization you may want to consider for your copy of the program. You can do this by modifying the constant (.75) in the statements on lines 630 of fig. 5. This value is a decimal hour representation of the half-width of the grey-line range. Changing these constants to .5 would give a ± 30 -minute tolerance for grey-line reporting. There's no reason to keep the test ranges symmetrical or even equal. You might benefit by skewing these tests to reflect your own preferences or station capabilities.

Once you start modifying PATHFINDER to suit your preferences, you'll appreciate the structured form of its code. There are lots of little program blocks defined as subroutines which are executed by the main program or by other subroutines. There might be a little more code required to do some functions than with a GOTO, but

FIGURE 6

```

PATHFINDER menu prompts and their functions
TOP menu:
Opt: 1=Input 2=Anal 3=Output 4=File 5=Quit
1 goto set INPUT menu
2 goto select ANALYSIS menu
3 goto select OUTPUT menu
4 goto select FILE function menu
5 QUIT the program

set INPUT menu:
Opt: 0=Top 1=Date 2=Flux 3=SSN 4=Target 5=Home
0 return to TOP level menu
1 change the DATE
2 change the solar FLUX
3 change the SUNSPOT NUMBER
4 change the TARGET coordinates
5 change the HOME coordinates

ANALYSIS select menu:
Opt: 0=Top 1=B/D 2=Grey 3=MUF
0 return to TOP level menu
1 report path BEARING and DISTANCE
2 report the endpoint GREY-LINE conditions
3 goto the MUF selection menu

MUF selection menu:
Opt: 0=Top 1=Short 2=Long 3=Radial
0 return to TOP level menu
1 project SHORT path hourly muf
2 project LONG path hourly muf
3 project RADIAL muf

FILE function select menu:
Opt: 0=Top 1=B/D 2=Grey 3=Target
0 return to TOP level menu
1 print global BEARING and DISTANCE report
2 print global GREY-LINE condition report
3 load TARGET location from file

```

PATHFINDER menu prompts and their functions.

FIGURE 7

```

PATHFINDER data prompts
PREFIX TO SEARCH FOR
enter a prefix to find for a new target
<CR> if OK, N for NEXT, else to QUIT
enter: a carriage return to accept this location
      "N" to reject this location and see others
      any other character returns to TOP level menu

What GMT hour for display
enter the time for a radial projection
(decimal hours)
1 Hop = 2488 mi (4000 Km). Long Path beyond 5
How many hops for display [0.1 to 9.9]
enter number of hops to use for radial path length
(decimal values ok)

Month number
enter the month number (1 to 12)

Day of month
enter the day of the month (1 to 28, 30 or 31)

Solar Flux [64 to 301]
enter a value for solar flux

Sun Spot Number [0 to 250]
enter a value for sunspot number

Target Latitude [- south, 89.9 max]
enter the target latitude in decimal degrees and then

Target Longitude [- east]
enter the target longitude in decimal degrees

Home Latitude [- south, 89.9 max]
enter the home latitude in decimal degrees and then

Home Longitude [- east]
enter the home longitude in decimal degrees

```

PATHFINDER data prompts.

FIGURE 8

```

PATHFINDER messages
Welcome to PATHFINDER-85
COPYRIGHT 1987 by Ronald C. Todd
PATHFINDER login and copyright message

ERROR
error message, occurs for several situations

Found: XVI in Lower Hattrap
requested prefix found

NOT Found
requested prefix not found

```

PATHFINDER messages.

FIGURE 9

```
GENDAT menu and data prompts

GENDAT MENU:
Opt: 1-Add 2-Edit 3-Insert 4-Delete 5-New 6-EXIT
1 ADD records to end of file
2 EDIT an existing record
3 INSERT records in middle of file
4 DELETE an existing record
5 initialize a NEW data file
6 generate the key file and EXIT the program

<CR> to Continue, else Done
enter a carriage return to continue with function,
otherwise return to menu

EDIT PREFIX:
enter the prefix you wish to edit

ADD AFTER PREFIX:
enter the prefix you wish to insert records after

DELETE PREFIX:
enter the prefix you wish to delete

D to Delete, else Reject
enter a 'p' if you really want to delete this record

Prefix
enter the record prefix

QTH
enter the record location name

Latitude
enter the record latitude in decimal degrees

Longitude
enter the record longitude in decimal degrees

<CR> if OK, R to Redo, else QUIT
enter a carriage return to accept input data
an "R" to redo the input data
otherwise return to function

<CR> if OK, N for NEXT, else to QUIT; B5
enter a carriage return to accept record found
an "N" to look for next occurrence of same prefix
otherwise quit the search and function
```

GENDAT menu and data prompts.

the partitioning of tasks in this manner means that debugging is easier and utility will be greater. I strongly suggest that you retain this design for your own revisions.

les Menus

Some of the original PATHFINDER users asked me to explain the menu functions. In fig. 6 you'll find a display of each of the menu prompts, along with a brief explanation of the function of each selection. A summary of the data prompts PATHFINDER uses is given in fig. 7 along with a description of what each means and, where significant, the data type expected. In fig. 8, you'll find the messages and a description of their meanings. Figures 9 and 10 give the menu functions, data prompts and messages for GENDAT. I'll be glad to answer all requests for more information accompanied by an SASE.

One other shortcoming of PATHFINDER, alluded to briefly in my original article, is error trapping. To keep the program to a reasonably publishable size, error trapping on most inputs has been minimized. This may generate some problems upon entering polar coordinates for one or both of the path end points. The solution in this case is to limit all latitudes to a magnitude of 89.99; this will be sufficiently close (0.69 miles from a pole) for most applications. In most instances, the likelihood of divide by zero and out-of-range errors have been minimized through the use of suitable decision gates in the algorithms. If you do find situations that generate errors not trapped by the code, please forward these to me. I'll

FIGURE 10

```
GENDAT messages

... PLEASE CHECK DATA ...
check input data before writing to file

END of FILE
end of file message

Found: XYI in Lower Hattrap Lat= 45 Lon=50
display of requested record found
```

GENDAT messages.

be glad to report them along with suggested code revisions. If there's sufficient interest, I might be talked into organizing a PATHFINDER user's group dedicated to maintaining and supporting the program.

Watch your language

All listings in this article are presented in Microsoft Extended Basic-80®, for a CP/M® operating system. This is a powerful and rather universal programming language, but it may have some features and syntax not shared with other BASIC dialects. Some of the constructs and statements which might not be included or may work differently in your BASIC are the DIM, DEFINT, ELSE, RESTORE, and ON GOTO/GOSUB. Your printer and disk access functions may require different approaches, but in general can be easily converted.

Several dialects of BASIC do not implement the ELSE clause for an IF/THEN construct; in that case you should place the statements executed by the ELSE condition on an intermediate line and then replace the ELSE with a GOTO branch past the intermediate line which contains the operations called for by the ELSE in this program. I normally increase the line number of the intermediate line by 5 from the source line when this is necessary. In summarizing conversions, it's best to keep your BASIC manual handy and refer to it whenever you have a question.

This version of PATHFINDER has been submitted to the ARRL Program Exchange. I would appreciate any suggestions you have for upgrades and further extensions to the program.

Thanks to all who have helped make PATHFINDER a viable reality by offering their comments and critiques.

For more updates to PATHFINDER see page 58. Ed.

references

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4. Wayne Overbeck and J.A. Steffen, *Computer Programs for Amateur Radio*, Hayden Book Company, Hasbrouck Heights, New Jersey, 1984.
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Article E

HAM RADIO

Answers to some common questions about PATHFINDER

Line 1200: The back slash "\ " is the integer division operator. It is used to assure an integer index for the array MOUT(). If your language does not support this feature then force the result of a normal division via the INT function: MOUT(INT(A0/10)) = J9.

Line 3420: This is recursive code, not an infinite loop. The line serves to force all computed longitudes into the range $-180 < = LON < = 180$. If the LON is outside the range, then 360 degrees (P1) is added or subtracted and the test repeated. When the LON is in range, execution passes on to line 3430.

Lines 8300 and 8320: These lines were referenced in the text of the article and several have found that 8320 does not exist in the listing, while 8300 is actually the start of the SSN input routine. This mixup is in the article text and not in the listing. The text should refer to lines 8400 and 8420 respectively.

Lines 300, 1040, 1160, and 1170: The STEP option on the FOR loops is a way of controlling both the increment value and the maximum iterations of the loop. The test and increment values for the loop control variable are set up to provide two MUF values per output line.

Updates to PATHFINDER release 1.10

Incorporate the following changes into your program as well as making the changes noted in the grey-line enhancements in fig.2 of PATHFINDER-Part 2. **30 'MICROSOFT BASIC version, Release 1.15, 5/12/88**

```
2040 IF K9(I) > 23.99 THEN 2100 ELSE IF SS(I) < SR(I) THEN 2060
```

```
4020 M9 = 1 + 2.5 * M9 * SQR(M9): IK = INT(G1/P5) + 1: L = 1 / (2 * IK)
```

These revisions will correct some PATHFINDER problems. Here is a new proof simulation which, if everything matches within 1.0 MHz, will demonstrate correct function.

Date is: Dec 21

Solar flux = 150.0 Sunspot number = 104

Home QTH: Lat = -87.0 Lon = 130.0

Target QTH: Lat = 80.0 Lon = -50.0

Path bearing = 0 degrees

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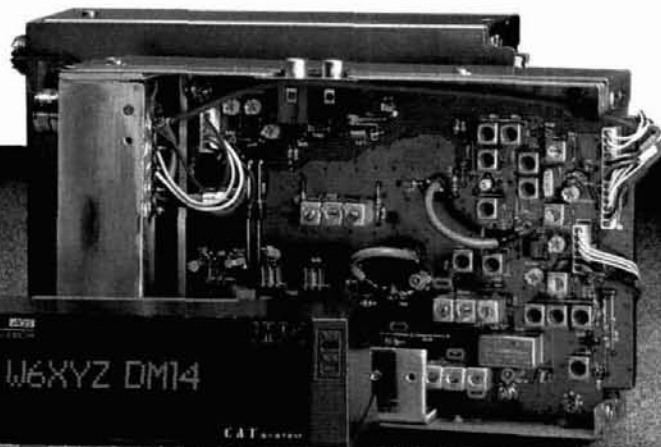
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Simple geometry
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impedance match device

The Amateur bands below 30 MHz are becoming crowded; consequently, many operators are moving to the VHF/UHF spectrum.

With higher frequencies come shorter wavelengths, distributed components, and shorter antennas. Shorter wavelengths allow for easier impedance matching between the transmission line and the antenna, or between two transmission lines of different impedances.

In the mid-fifties an article about a device called a G-line appeared in *Radio and Television News*. It consisted of a single hard-wire line with launchers to match impedances at each end. The G-line never became very popular, but the launcher has some nice qualities at higher frequencies. It looks like a funnel and works on the same principle as coaxial cable.

The impedance of coax is found by the ratio of the center conductor diameter to the inside diameter of the shield, using the following formula that disregards the dielectric:

$$Z = 138 \text{ Log } (D2/D1) \quad (1)$$

Where D2 is the inside diameter of the shield and D1 is the outside diameter of the center conductor.

By changing the ratio of D1 to D2 you change the impedance of the transmission line. If the transmission line impedance changes gradually, say over a quarter wavelength, the transition won't create a standing wave sufficient to cause appreciable loss. In short, you can match two impedances with minimum loss. This same concept is used in the G-line launcher.

The wavelength at 450 MHz is 66.66 cm, just 2/3 of a meter. A quarter wave length is only 16 cm. This short wavelength allows you to use the distributed compo-

nents of coax to make an impedance transformer that will serve for any frequency within that Amateur band.

For example, if you have a helix antenna and a length of 50-ohm coax cable, the input impedance of the helix is approximately 140 ohms. The mismatch that would accompany a direct connection would cancel out the antenna's gain. If you choose to use a quarter-wavelength coaxial transformer for matching, it would need a characteristic impedance of:

$$\begin{aligned} Z &= \sqrt{(Z1 \times Z2)} \\ &= \sqrt{(50 \times 140)} \\ &= 83.66 \text{ ohms} \end{aligned}$$

which is not a standard value. By using a launcher, you can effect a more efficient match between the cable and the helix.

The launcher dimensions include the input diameter, output diameter, and length. The length is not critical — but it should be longer than a quarter wavelength at the lowest frequency of operation. The two diameters are a function of the impedances.

The input diameter, for a 50-ohm cable is found as follows:

$$Z_{in} = 138 \text{ Log } (D2/D1)$$

$$\text{Let } D1 = 1$$

$$\text{Then } 50 = 138 \text{ Log } D2$$

$$2.303 = D2$$

The narrow end of the cone is 2-1/3 times larger than the wire of the helix antenna or the center conductor of the cable.

The output diameter of the cone for a 140-ohm antenna is as follows:

$$Z_{out} = 138 \text{ Log } (D3/D1)$$

$$\text{Let } D1 = 1$$

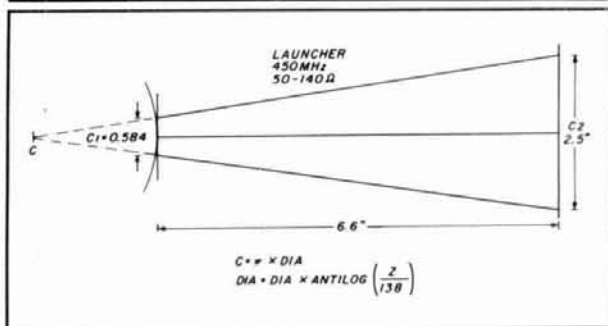
$$\text{Then } 140 = 138 \text{ Log } D3$$

$$10.33 = D3$$

The wide end of the cone is 10-1/3 times the wire of the helix antenna or the center conductor of the cable.

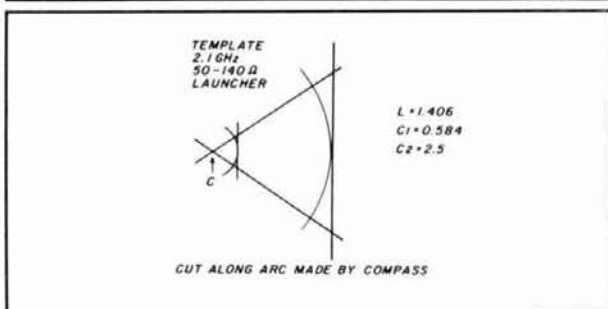
Use the information above to construct the launcher. First draw a template as shown in fig. 1. I used No. 12 AWG wire (diameter = 0.08081 inches) for D1. Cut along the curved lines and roll it onto itself to form the cone. If you have a compass with a 9-inch span, scribe

FIGURE 1



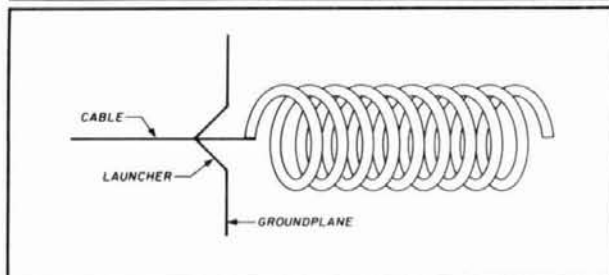
450-MHz roll-your-own launcher template.

FIGURE 2



Template for 2.1 GHz 50-140 launcher. Cut along arc made by compass.

FIGURE 3



Helix antenna with launcher.

both ends as I did in the 2.1-GHz version in **fig. 2**. It will give the cone sides of equal length.

Purists will argue that the cone should be logarithmic like an old automobile horn. But you're working at the narrow end of the horn, and at that point the lines are almost straight.

One additional thing: if you're building a helix, the launcher diameter must be smaller than the helix diameter or the ground plane will fail. **Figure 3** shows the helix with launcher attached to the ground plane.

To test the idea, I built a helix antenna for 2.1 GHz and attached the launcher at the feedpoint. Return loss measurements of 18 dB indicate the antenna system works well.

Article F

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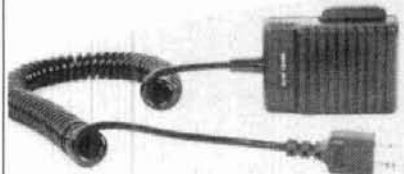
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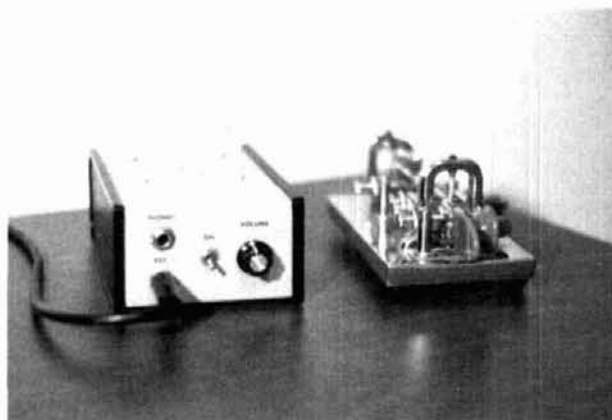
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1	1k
1	1M
2	220
1	470k
1	4k
1	39
1	10
1	270
2	15k

Potentiometers

1	10k audio taper
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ICs

1	LM386 (Radio Shack no. 276-1731)
1	MC3340A/ECG1829
1	LM741 (Radio Shack no. 276-1601)

Miscellaneous

2	9v Battery
2	Phone jack
2	Battery connector
1	DPST switch
1	3" speaker
1	Enclosure (Ten Tec JG-4) 4" x 2-1/4" x 6"
3 (optional)	8 pin DIP socket
	Perf board (Radio Shack)
	Fuse clip (Radio Shack)

Capacitors

4	400 μ F (electrolytic)
1	10 μ F (tantalum)
2	01 μ F (disc)
1	1 μ F (disc)
1	2 μ F (disc)
1	002 μ F (disc)

resistance. The voltage divider consists of the 220-ohm feedback resistor (R1) and lamp. It feeds back a higher proportion of the signal to the inverting input decreasing the closed loop gain. The amplitude decreases and is regulated. In normal operation the lamp's light will be invisible. Active devices in the op-amp are operated in the linear region yielding a single-tone sine wave.

Other audio amplifier circuits drive into saturation to regulate the amplitude. This causes the sine wave to be "squared off", generating distortion. Circuits using the 555 timer IC produce true square waves and have particularly raspy tones.

Oscillation frequency is controlled by the dual RC network in the noninverting feedback loop. Two 15k resistors and capacitors (C1), made up of three 4700 pF and one 680 pF disc ceramic capacitor, set an 800-Hz tone. These values can be changed to suit your preference. The resistors and capacitor don't have to be matched.

Keying the circuit in fig. 1 through the power leads is *not* recommended. A chirp would be produced as the lamp comes up to temperature. Let the oscillator run continuously and key its output signal with the electronic attenuator, IC2 (Motorola part MC3340P — also available as ECG829), in fig. 2. A key in the gain control input does a nice job. Shaping is controlled by the 4k and 0.2 μ F RC time constant; during key up



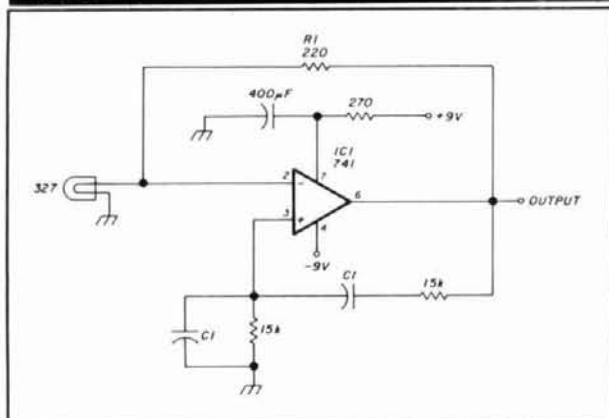
A CODE PRACTICE OSCILLATOR

Many code practice circuits have been published. Most will do an acceptable job, but tend to have a very rough "buzz saw" tone. They don't sound anything like a CW signal received off the air. This code practice oscillator has a pure sine wave 800-Hz note. It's a joy to use.

Circuit details

To obtain a pure tone, I used an audio oscillator that generates a sine wave with low distortion. In the circuit in fig. 1, an incandescent lamp-type 327, 28 volts at 40mA controls the feedback to the inverting input of a 741 operational amplifier. It regulates the signal amplitude to 5 volts peak-to-peak. The lamp glows brighter if the amplitude rises, increasing its

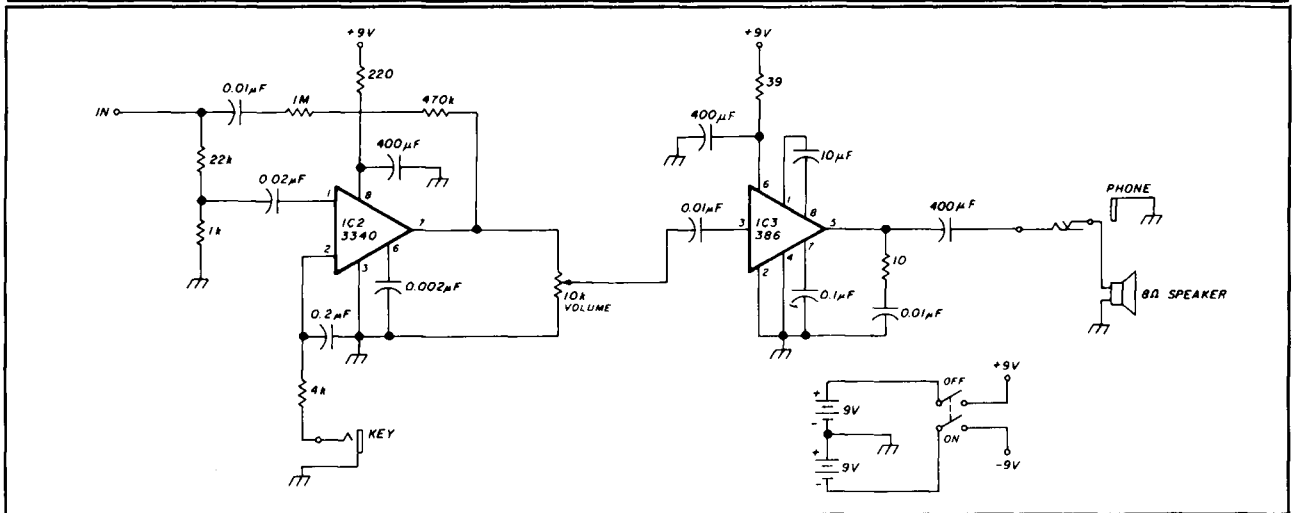
FIGURE 1



Oscillator circuit.

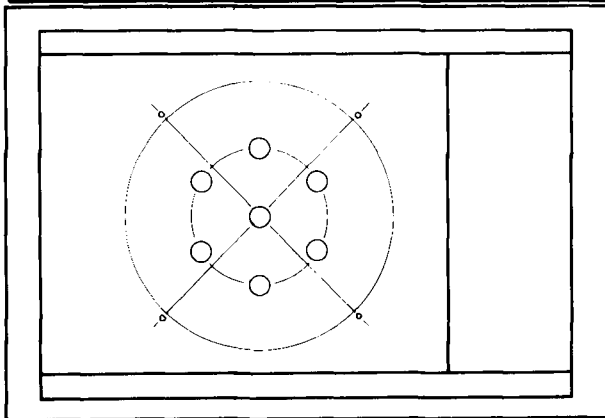
By John Pivnichny, N2DCH, 3824 Pembroke Lane, Vestal, New York 13850

FIGURE 2



Keying circuit and power amplifier.

FIGURE 3



Top cover.

this part provides 60-80 dB attenuation. This may not be enough to completely eliminate a backwave signal. A feed-forward path using a 0.01 µF capacitor, 1 meg resistor, and a 470k resistor in series cancels any residual backwave signal. Note that the signal going through IC2 is inverted while the feed-forward signal is not; the two cancel out during key up. During key down IC2 provides 13-dB gain and can accept a maximum of 0.5 volt peak-to-peak signal at its input (pin 1). The resistive voltage divider at its input decreases the oscillator amplitude to an acceptable level.

Power amplifier IC3 is a conventional 386 circuit.^{2,3} There is enough power gain to drive headphones or a small speaker. Figure 2 shows the keyer and audio amplifier circuits. Two 9-volt transistor radio batteries supply power. The positive supply is decoupled at each IC. (This may be unnecessary as all circuits are very stable.)

Construction

All components are mounted on a 1-3/4" × 3" piece of perfboard. The lamp is mounted with a single fuse clip connecting it to the outside of the base, and a No. 30 gauge wire is soldered to the base center contact. The two batteries are held in place with spring clips fastened to the bottom of the enclosure with 4-40 × 1/4" machine screws. All other components are attached to the circuit board by their leads. I used insulated No. 30 gauge wire for the interconnections.

The box is 4" × 2-1/4" × 6" with a gray finish and black plastic side panels. A 3" diameter speaker is fastened to the top cover. Seven 1/4" holes, drilled as shown in fig. 3, form a speaker grill. There are also four 1/16" holes for speaker mounting machine screws. The front panel holds two 1/4" phone jacks for the key and earphone plugs, a DPST power switch, and the volume control. Dry transfer lettering with a protective coat of clear shellac completes the job. See the photograph for details.

Operation

Keying is done with a hand key, keyer, or semi-automatic bug. The built-in speaker and batteries make this oscillator compact, easy to use, and portable. Why not build one up for your next project?

References

1. Tom Schultz, "Audio Oscillator," *QST*, "Hints and Kinks," November 1974, page 43.
2. Rick Littlefield, K1BQT, "Construct an Audio Amplifier...", *QST*, April 1983, pages 28-31.
3. J. Rusgrove, "A General Purpose Audio Amplifier," *QST*, November 1976, page 32.



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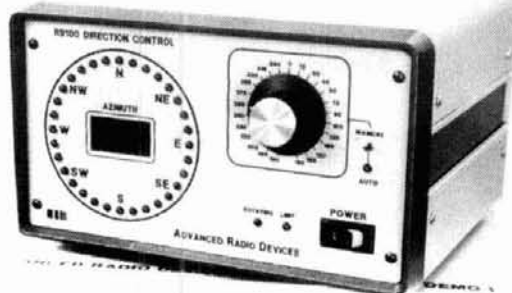
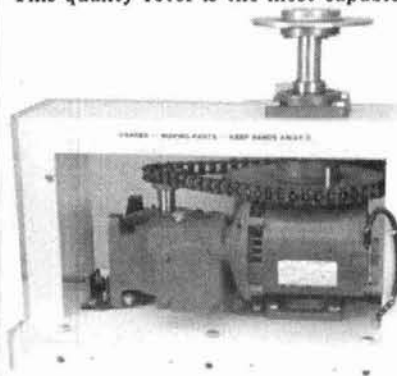
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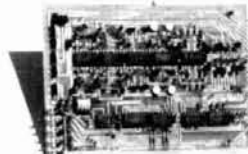
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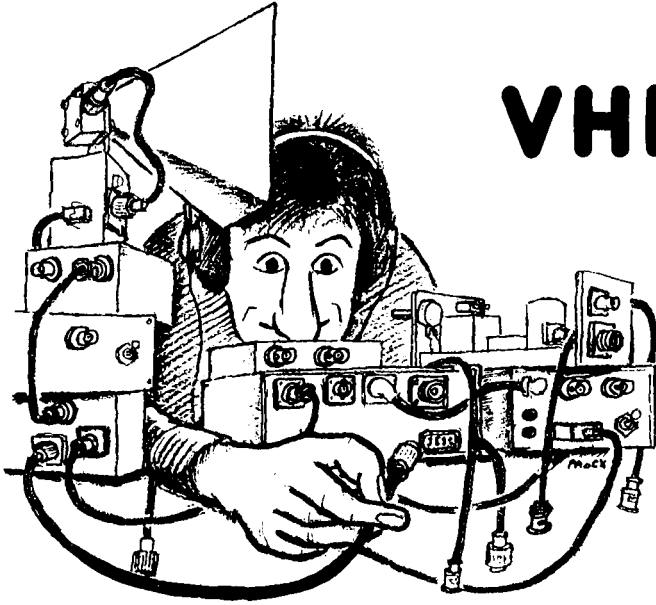
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VHF/UHF WORLD

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IMD and splatter

Interference has always been one of the greatest impediments to communications, regardless of frequency. If an Amateur with a strong signal transmits right on a frequency where a weak signal is present, there is virtually no way you can copy the weaker signal unless the stronger station stops transmitting.

But, interference isn't confined to the simple case described above. Often there are other circumstances like IMD (intermodulation distortion) — often referred to as splatter on SSB. The latter may be transmitted, or locally generated in the receiver.

This month I'll review the subject of IMD/splatter, answer some of the most often asked questions, and discuss some recommendations and test methods.

CW transmission

Using CW provides a partial solution to the interference problem. Even if two signals are on exactly the same frequency, you can achieve partial copy of the weak signal when the strong signal is "key up." Also, if a weak signal is on a slightly different frequency from a strong one (perhaps as little as 1.0 kHz away), and the strong signal is not blocking your receiver, you may be able to separate

the signals if you have a good narrow-band i-f filter (typically 500-Hz bandwidth) in your receiver.

There is a very basic reason why CW signals can be so easily separated. A good clean CW signal occupies very little bandwidth — less than 500 Hz, as shown in **fig. 1A**. This is only true if the oscillator in the transmitter is very stable and doesn't have any "phase noise."

Phase noise is a form of frequency modulation that is often superimposed on the carrier frequency. As a result, a transmitted signal is broadened or spread out in frequency (see **fig. 1B**). This phenomenon is particularly evident in the modern-day synthesized transceivers. I often refer to phase noise as the "aurora" affect. If you tune a few kilohertz off the carrier of a CW signal with phase noise, it sounds like keyed white noise which is similar to the signal returning from the auroral reflection.

Further complicating this phenomenon is that the local oscillator in your receiver may also have phase noise, exacerbating the problem. It will be difficult, if not impossible, to determine whether the transmitter or the receiver, or both, are the culprits! For those who want more information on this communications bugaboo, I'd recommend reading reference 1.

SSB transmission

As if the problems of CW transmission weren't bad enough, enter an SSB transmitter and you have a whole new ballgame. By nature an SSB signal has a broad bandwidth, typically 2-3 kHz at the half-power point, when carrying voice intelligence.

In the good old days, SSB signals were generated by the phasing method because it was low cost and had good fidelity. Phasing exciters characteristically have wider bandwidth because the filtering and phasing required is more complex.

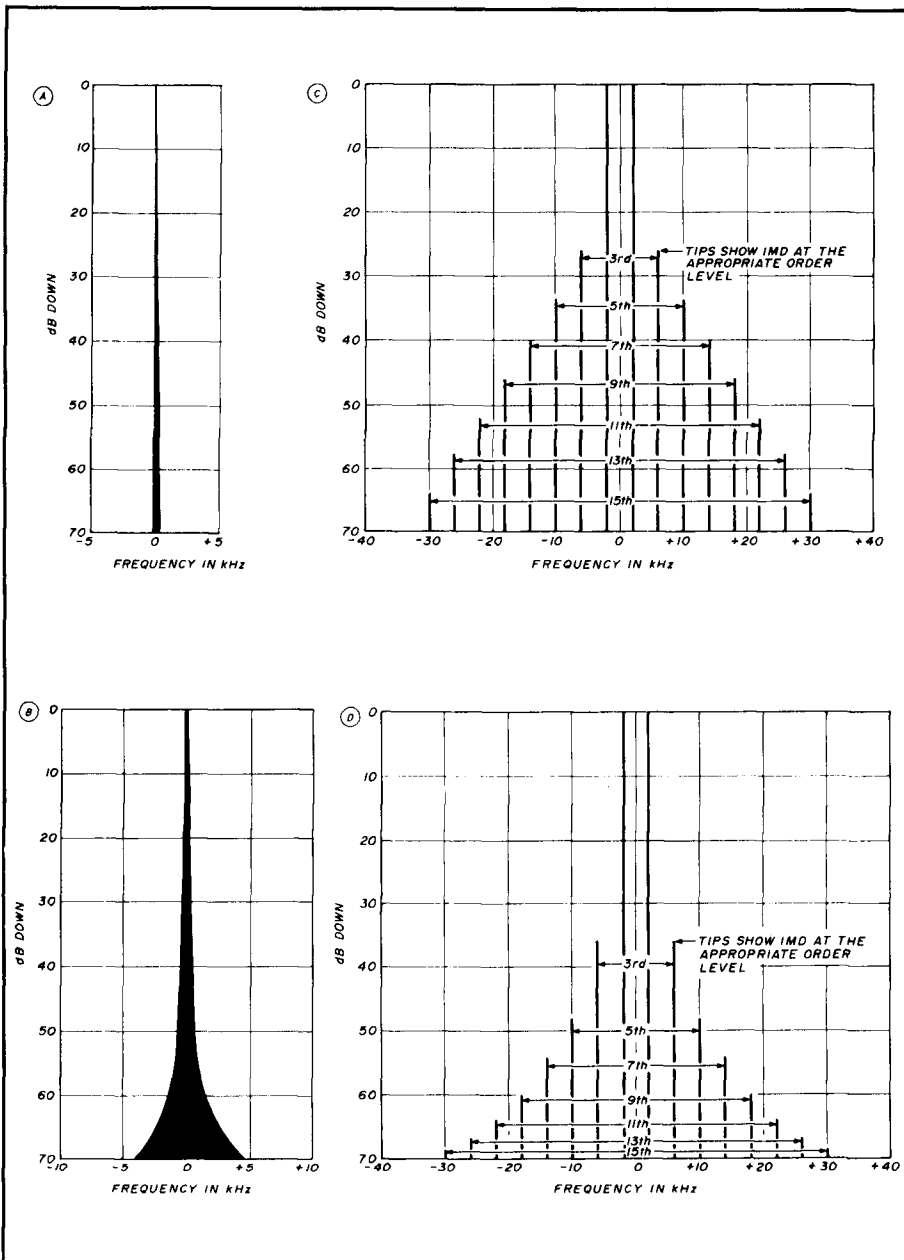
Most modern exciters generate SSB by the rf-filtering method which employs well-controlled crystal band-pass filters. However, even these filters are seldom specified over more than a 40-dB range.

The local VHF/UHFers can tell when I alternate between my phasing and filter SSB exciters. The phasing exciter has good audio fidelity, but the IMD outside the passband is at a higher level. The filter exciter has poorer audio fidelity, but outside the passband IMD drops off at a faster rate.

What most Amateurs tend to forget is that SSB signals, by their very nature, have "controlled" IMD. Amateur SSB exciters and power amplifiers are often specified to have a typical IMD specification — 26-30 dB at a specific PEP output level. This means that the third order IMD products (the ones generated closest to the desired signal but outside the 2.5-3 kHz passband), are only 26-30 dB below the peak power level specified. Higher order sidebands are also present, but usually at a lower level.

Figure 1C puts all this in perspec-

FIGURE 1



(A) The output spectrum of a pure CW signal.
 (B) The output spectrum of a typical CW signal with phase noise.
 (C) The output spectrum of a clean SSB signal from a commercial amplifier.
 (D) A typical Amateur SSB transmitter.

tive. It shows the typical output spectrum from a "commercial quality" filter-type SSB transmitter when modulated by two identical level audio tones, one near 500 and the other near 2500 Hz (adapted from reference 2). Remember that this spectrum display is typically 6-10 dB better than the average Amateur transmitter.

Referring to fig. 1C, note the high

level of rf at the 3rd order level — typically 36-dB down. Consequently, there will be rf energy outside the normal 2-3 kHz passband that will be only 36-dB below the carrier peaks, or about one four-thousandth of the peak power. Not bad if the station is only 25-30 dB out of the noise, but very objectionable if it's 40-60 dB out of the noise.

What about the higher order sidebands? The 5th, 7th, and 9th order IMD products are still only down 48-60 dB. They will be very noticeable on a strong local station which is typically 60-80 dB out of the noise!

To the average HFer, these problems may be an annoyance. With heavy interference, local noise, and intermittent operation (like a "DX pileup") you can learn to "live with it." However, to the VHF/UHFer who often listens on a relatively quiet band over a limited frequency range, IMD can be difficult to tolerate.

SSB splatter

So far I've been talking about the idealized transmitter case. What's it like when the IMD levels of an SSB transmitter are at Amateur specifications? Worse yet, what happens when an Amateur is trying to "eek out" the last bit of transmitted power by shouting into the microphone or turning the gain control up too high?

Figure 1D shows one possible spectrum display. This is a typical Amateur transmitter output spectrum at rated power output. Note that the 3rd order IMD products are only 26-dB below the peak power level. Furthermore, the 9th order products are 46-dB down, 14-dB worse than the commercial transmitter! Remember that if the transmitter is driven above these levels, the IMD will increase dramatically.

Why is this true? The linearity of a transmitter is limited by the ability of each stage to accurately reproduce and amplify the input signal. Each stage, usually a vacuum tube or solid state device, has a finite output power level beyond which it will generate distortion. Exceeding this level results in high levels of IMD and splatter.

Transmitting devices

Let's compare some typical transmitting devices. Vacuum tubes have been around a long time and maintain a good reputation when used as rf power amplifiers. RF transistors are in wide use, although they are often

TABLE 1

This table shows some of the most popular VHF/UHF high power transmitting tubes used by Amateurs. The ratings are extracted from manufacturers' data sheets. See text for further explanation.

Tube type	Dissipation in watts	Peak envelope power output	IMD specs	Remarks
Triodes				
3CX400A7/8874	400	590	35	
3-400Z/8163	400	590	28	
3CX800A7	800	750	36	
3-1000Z/8164	1000	1080	29	
3CX1500A7/8877	1500	2000	38	
8938	1500	2000	44	
Tetrodes				
4CX250R/7580W	250	470	23	
8930	350	350	27	Formerly DX393
7650	600	680	31	
4-1000/8166	1000	1540	NA	IMD Estimate 25 dB
4CX1000A/8168	1000	1400	23	
7213	1500	1000	NA	IMD Estimate 25 dB
4CX1500B/8660	1500	1500	43	
NA: Not available				

unfairly targeted as "splatter generators." More on this shortly.

Operating each stage of a transmitter in class "A" would be ideal for linear operation, but the power consumption would increase. The power dissipation of each stage would also be high, making the cost of the appropriate high power amplifier devices prohibitive. On the other hand, operating each transmitting stage in class "C" would raise efficiency, but distortion would be prohibitive.

As a result, most vacuum tube amplifiers are operated in class "AB" with moderate idling current. Vacuum tubes are usually large and, if they can't dissipate heat easily by themselves, heat dissipation can be assisted by a fan or blower.

Cooling solid-state devices with their very small geometry is still a problem, but one that is improving. Large heat sinks and special compounds are used to thermally bond the devices to the heat sink. Also most solid-state devices are operated in class "B." However, they are more prone to distortion.

Another reason vacuum tubes are so linear is that they operate with high voltages on the anode. Consequently,

there is a large voltage difference between the typical operating voltage on the anode and the minimum voltage across the anode when saturation occurs. If you go back to old vacuum tube literature you'll find lots of discussion about "load lines." In the typical vacuum tube application the load line operates over a very wide voltage swing before saturation and distortion occurs. Furthermore, vacuum tubes usually operate with output impedance levels of 1-5,000 ohms. This is a moderately easy impedance to match to 50 ohms; it's often done with a pi-network. As a result, impedance matching losses are usually low and efficiency is high.

Contrast this with the typical solid-state power amplifier used by Amateurs. It most often uses transistors specified for 12-14 volt operation because this is the voltage usually used in mobile operation, and therefore in Amateur shacks. These devices typically saturate at 1-2 volts, so the load line operates over a very narrow voltage range.

The operating impedance levels of the typical rf solid-state transistor are low, usually 1-10 ohms! This makes the matching networks more complex

and lossy. At UHF frequencies the parasitics of the components themselves become a major problem.

The use of higher voltage transistors like the 28-volt types will improve linearity, but require higher supply voltages at lower current. The development of MOS (metal oxide semiconductors) power FETs is a promising field. These devices usually require a 25-60 volt supply, although some lower-power types operate at 12-14 supply voltages.

Proper amplifier operating parameters

Now let's look specifically at power amplifiers. It should be obvious why just about all Amateur amplifiers, especially the commercial types, operate in linear service. Linear amplifiers are less likely to abruptly change power and can be used on any emission type: CW, FM, SSB, or ATV.

Vacuum tubes are still the favorite source of linear power, especially when good IMD and power levels over 100-200 watts are desired. But, the fact that an amplifier uses a vacuum tube is no guarantee that it will be linear. Certain operating parameters must be met. Many of them are described in references 3 and 4. Furthermore, what is often ignored is that for good IMD performance, the type of tube selected is often more important than the operating parameters. If the tube you choose isn't specifically designed for linear service, you probably won't obtain good linear output characteristics — regardless of the operating parameters and circuitry employed.

Generally speaking, at VHF/UHF frequencies, tetrodes have the highest power gain and are usually operated in the grounded-cathode configuration. However, the newer high-mu triodes driven in the ground-grid configuration, while having less gain, will generally deliver the best IMD performance.

Table 1 shows the expected linear performance from some of the most popular tubes Amateurs use. Data has been gleaned from manufacturers data sheets and literature.^{5,6}

mation on older tubes (prior to 1970) is almost nonexistent. From the table, it is obvious that the newer high-Mu triodes generally have better IMD performance. Additional parameter information is available in reference 3.

One further caution. The IMD shown in table 1 is an optimized target figure and will vary somewhat with different tubes. These numbers were probably derived under tight laboratory conditions with good instrumentation.

Table 1 is by no means complete. Always get the exact parameters directly from the manufacturers data sheets, not "Joe Ham" down the street. Deviating from the specific operating voltages shown on these data sheets will probably degrade the IMD.

If a tube is driven to higher power levels than shown, the IMD will drop accordingly. As a rough rule of thumb, every time the power output is doubled, the IMD will degrade by at least 6 dB. Going above the output power shown on table 1 is strongly discouraged, unless you want to severely

shorten the life of your tubes. Furthermore, you'll gain the ire of every VHF/UHFer in your area who'll be telling you how badly you're splattering.

Solid-state power amplifiers are popular, especially those delivering 10-160 watts. They are generally small in size and only require a single power supply voltage. Reference 7 describes them in detail, along with recommended circuitry. As stated above, the 12-14 volt transistor types are the most common. Some precautions are advised. The power supply should be fairly well regulated and, preferably, adjustable.

Most solid-state amplifiers are specified to operate at approximately 13.5 volts. Dropping the power supply voltage to 12 volts will usually drop the output power by 10-20 percent! Likewise, the IMD will severely degrade.

Pay special attention when wiring the power supply to a solid-state power amplifier. Large diameter wire, no. 14 or larger AWG, is recommended since these amplifiers draw from 5-20A. Small diameter wire will

cause a large voltage drop on the power supply lines, with a commensurate decrease in output power and IMD as described above.

As mentioned earlier, solid-state power amplifiers have developed a bad reputation with regards to splatter. There are many reasons for this. As I noted above, the power supply and supply voltage are sometimes to blame. But, the biggest offender is probably the user and his or her interpretation of the manufacturers' specification.

For example, a typical amplifier specification may say "100 watts output with 10 watts of drive." This implies that the amplifier has a true gain of 10 dB.

In reality, the 100 watts of output power may be the maximum output power possible from the amplifier, not the maximum linear output power. Also, the gain may be much higher at the lower output power. Lastly, you may be overdriving the amplifier.

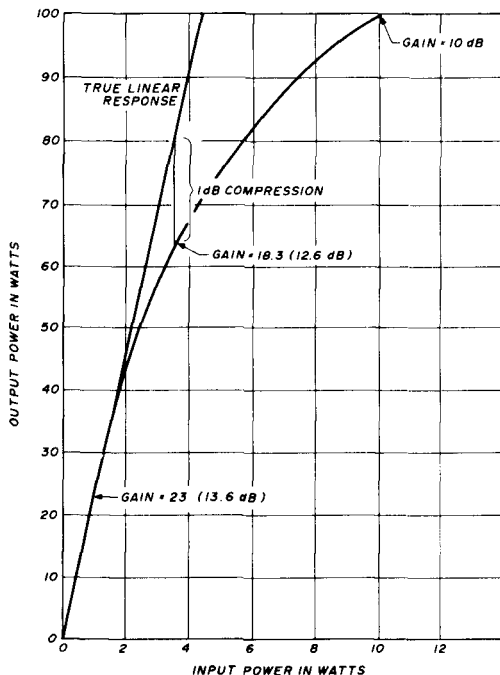
Testing and evaluating power amplifiers

Up to now I've been describing operating parameters. Now let's dig in and see how to test, evaluate, and operate a linear power amplifier. Then you'll be able to better apply this information to your own station.

To better illustrate the point of linearity and specifications, I've plotted on fig. 2 the true output versus input power on a typical Amateur commercial 100-watt VHF solid-state power amplifier. Figure 2 shows that an input power of 1.0 watt yields an output power of approximately 23 watts — a gain of 23 or 13.6 dB. At 3.5 watts input, the output power is approximately 64 watts, a gain of 18.3 or 12.6 dB. Finally, at 10 watts input, the output power is approximately 100 watts; the gain is 10 dB.

Note that the gain isn't constant. What went wrong? The answer is nothing. This output versus input characteristic is typical of the solid-state power amplifiers used by Amateurs. They are linear, but only up to a point.

FIGURE 2



The graph shows the input versus output power from a typical VHF Amateur commercial amplifier. See text for further information on how to interpret the results and perform your own tests.



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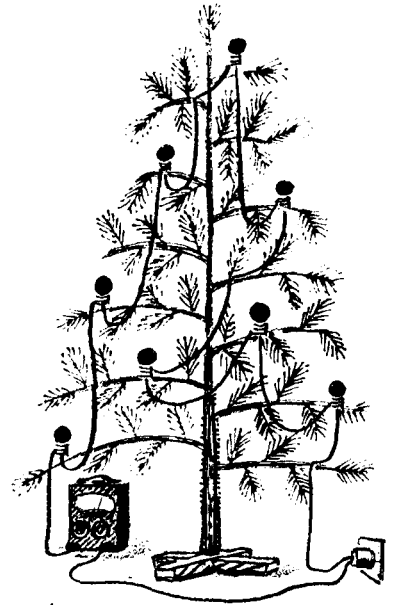
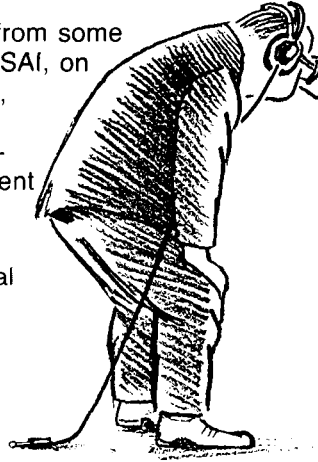
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In a true linear amplifier, a 1-dB input power increase would yield a 1-dB output power increase. In the case of solid-state power amplifiers, linear operation is generally acceptable up to the "1-dB compression point" — the output power level where the gain of the amplifier drops 1.0-dB below the low-power gain.

Said another way, the 1-dB compression point is the output power level where the amplifier output increases only 9 db for a 10 dB input power increase. Above this power level distortion and IMD increase rapidly.

Fine you say, but how do I test compression? The easiest way is to use two power meters, one at the input and one at the output of your amplifier (see fig. 3). Measure the output power at 5-10 different power levels. The greater the number of data points taken, the

the peak power to register, if in fact it ever does. This means that on SSB, the peak power you are running should never show on the meter. If it is, you're driving the rig too hard!

When using a typical power meter, you should be averaging about 25-30 percent of full linear power (1-dB compression point) capability. Never exceed 50 percent (see reference 7). Test your linearity, then advance the microphone gain on your exciter and observe the output power. If you ever reach a point where output power no longer increases with increasing microphone gain, back it down!

Say you have an amplifier that puts out 100 watts of linear power, after measuring it according to the methods described above. Set your gain control on the rig so that on average voice it is indicating 25-30 watts, as shown in fig. 4. This goes a long way towards

insuring that you are not splattering excessively and will still be transmitting full power on peaks!

If your power amplifier has too much gain (the most typical case) you'll have to be careful to keep the microphone gain turned down, or place an attenuator between the exciter and amplifier, or both. You can use a piece of RG-58 cable as an inexpensive moderate-power attenuator.⁸ At about 4-5 dB per 100 feet at 2-meters, you may only require 25-75 feet.

If you have ALC capability, use it! It's a great way to control the tendency to overdrive a rig, especially if the amplifier has too much gain.

Other tips

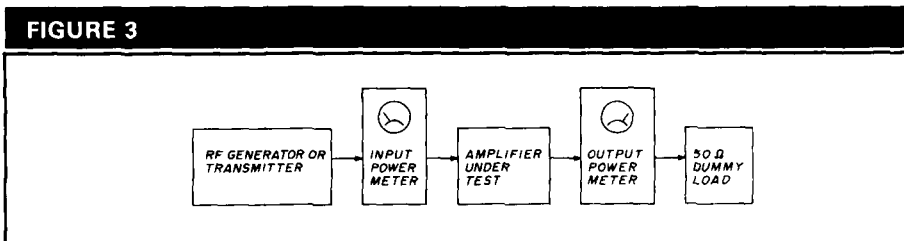
Never use an amplifier unless it's necessary. Remember the FCC regulation that Amateurs should use the minimum power required to maintain communications.

If you overdrive your rig, your signal may still sound great to the station listening to you! Try an A/B test. Switch your amplifier in and out, and have a local station observe the change in signal strength to verify that your gain increases by the number of dB expected from the power amplifier. Then have them tune off 5-10 kHz and repeat the A/B test to see if the IMD degrades with the power amplifier in line.

Remember that all IMD power is wasted and serves no purpose other than to cause interference to adjacent channels!⁵ Excessive power and overdrive, especially on solid state amps, can also cause premature death to the output devices.

Despite stories to the contrary, the gain of vacuum tube VHF/UHF amplifiers is finite, typically 10-17 dB. Don't expect a 10-watt exciter to drive a 1000-watt amplifier to full output power. You may still need a driver amplifier ahead of the final.

Test all new gear with a local. Problems such as misalignment and breakage can occur during shipment. Carrier suppression is sometimes a problem, but can usually be re-



This diagram shows a recommended test set up to measure the linearity of a power amplifier as described in the text.

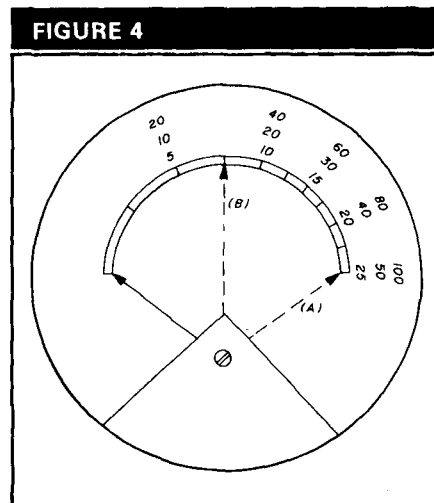
greater the accuracy. Plot the results as shown in fig. 2.

Next, draw the "true linear response line" from the origin as shown on fig. 2. The 1-dB compression point is the measured output power level which is 80-percent (-1 db) below the expected output power (64 versus 80 watts in fig. 2).

Power meters

There are several other things to remember when operating a linear. You must have a power meter; an external one is preferable. Without a calibrated power meter you'll never be able to determine if your equipment is operating properly.

There are several caveats when using a power meter. First, they all have a time constant. It takes time for



This diagram shows the face plate of a typical RF power meter. A is the key-down needle position for maximum linear power. B is the recommended needle position when operating SSB for same as described in text.

tweaked. In rare cases, power amplifiers may have to be re-peaked.

RF actuated power amplifiers can often cause a problem at lower power levels because they may not turn on properly. If possible, try to hard wire the switching on these amplifiers to the station or exciter T/R line.

RF compression is another topic that is really beyond the scope of this month's column. Suffice it to say that if you have it, try it, but only when necessary on weak signal paths. Adjust it carefully and don't use any more compression than necessary! Remember that rf compression significantly increases dissipation in the power amplifier, which could destroy or shorten device life.

Finally, for many years Vhf/UHFers have been gathering at conferences to shoot the bull, measure noise figures, and antenna gains. Maybe it's time we add a new wrinkle to these conferences by setting up workshops to test amplifier power and linearity.

Receiver considerations

So far I've concentrated mostly on the transmitter IMD. I feel that it's most often the culprit and is the easiest problem to deal with. This, of course, isn't always true.

Many of the transceivers used on VHF/UHF, and to a lesser degree those used on hf, have very poor dynamic range. This is especially true of those that were designed before 1985. Furthermore, transceivers and transverters often have poor sensitivity. The latter is not a problem on hf where noise levels are high. But, the typical 6-8 dB noise figures on 2-meters and above often require an external low-noise preamplifier. When such a preamplifier is added, the dynamic range of the receiver drops dramatically.

Low noise preamps don't usually suffer from IMD. However, they usually overdrive the rx following it. The rx has insufficient dynamic range and crashes. If you use an external preamplifier, configure it so that it can be easily bypassed especially if you suspect IMD.

Receiver IMD can usually be tested simply. If you place an attenuator ahead

of a receiver, the signal should decrease by the same amount of dBs as the attenuator. However, if the receiver IMD drops by a greater amount, some or all of the IMD is generated by the receiver.

As a rule of thumb, IMD that is generated in a receiver decreases 3 dB for every 1-dB decrease in signal level. A 3-10 dB 50-ohm attenuator pad is a nifty test device. If you suspect a station is causing IMD, note the signal strength and IMD level on the signal strength meter.

Next insert a 3-10 dB attenuator ahead of your receiver/preamplifier. The signal level should drop by the amount of attenuation introduced. If the IMD also drops the same amount, the transmitted signal is probably at fault. If the IMD level drops more than the amount of the attenuator, your receiver is partially at fault. If the receiver IMD drops 3 times the attenuator value, the IMD is probably all generated within your receiver.

You can try one final, simple test. By carefully watching a station on the signal strength meter, you can often see overdrive by observing how much the meter wiggles. A station that's clean will generally cause a typical S meter to move rapidly. A station hitting their transmitter too hard will cause the S meter to sort of hang near the same level because they are in compression.

Summary

This month's column was primarily devoted to improving linearity and decreasing IMD/splatter. Try never to run more power than required. Remember that a true linear doesn't exist. Sooner or later it will run out of gas as the power output is increased. Test your transmitted and received linearity as detailed above and, if you like, try some of the other suggestions I've made.

Note:

In reference 9, I described circuitry to obtain 28 volts from a 12-volt power supply, primarily for operating relays on portable operation. I've been informed that there is a commercial device already available — a Radio Shack Voltage Inverter, catalog number 22-129B.

Although it's shown as a 6-12 volt inverter, the instruction sheets clearly show how to use it for a negative ground 12-28 volt inverter. Many thanks to Bill Murray, K2GQI, for bringing this to my attention.

Important VHF/UHF events

- | | |
|----------------|---|
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1 UHF Contest
(70-cm and up)</i> |
| October 1-2 | <i>Mid-Atlantic States VHF
Conference, Warminster,
Pennsylvania (contact
WB2NPE/WC2K)</i> |
| October 9 | <i>Predicted peak of the
Draconids meteor
shower at 0900 UTC</i> |
| October 10 | <i>New moon</i> |
| October 20 | <i>Predicted peak of the
Orionids meteor shower
at 1400 UTC</i> |
| October 23 | <i>EME perigee</i> |
| October 22-23 | <i>ARRL International EME
contest, first weekend</i> |
| November 3 | <i>Predicted peak of the
Cassiopeids meteor
shower at 0245 UTC</i> |
| November 3 | <i>Predicted peak of the
Taurids meteor shower at
0300 UTC</i> |
| November 9 | <i>New moon</i> |
| November 16 | <i>Predicted peak of the
Leonids meteor shower
at 2000 UTC</i> |
| November 20 | <i>EME perigee</i> |
| November 26-27 | <i>ARRL International EME
contest, second week-
end.</i> |

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- A NEW CONCEPT IN REPEATER DESIGN, THE Hi Pro "E" IS AN EXPANDABLE REPEATER WITH THE FOLLOWING FEATURES: A BASIC REPEATER WHICH WOULD INCLUDE A COMPLETE RECEIVER, TRANSMITTER, COF, FRONT PANEL CONTROLS AND INDICATORS, LOCAL SPEAKER AND MIC JACK AND CAPABLE OF FUTURE EXPANSION. ALL HOUSED IN AN EXTREMELY RUGGED, ENCLOSED, 19-INCH RACK MOUNTABLE CABINET.
 - THIS SYSTEM CAN BE EXPANDED AT TIME OF PURCHASE OR CAN BE AN AFTER-PURCHASE ADD ON. THE ADD ONS ARE—HIGHER POWER, 110/220 VAC POWER SUPPLY, IDENTIFIER, AUTO PATCH, OR COMPUTER CONTROLLERS. IN ADDITION TO THESE ADD ONS AN ADDITIONAL RECEIVER AND TRANSMITTER CAN BE MOUNTED INTERNALLY FOR USE AS CONTROL LINKS, REMOTE BASE OR DUAL BAND OPERATION, ETC.
- AN EXTENSION PANEL IS AVAILABLE FOR LOCAL MONITORING OF THE REPEATER AND CONTAINS ALL NECESSARY METERING, STATUS LIGHTS AND INDICATORS. ALL ADD ONS ARE AVAILABLE FROM THE COMPANY AND ARE COMPLETE INCLUDING INSTRUCTIONS.

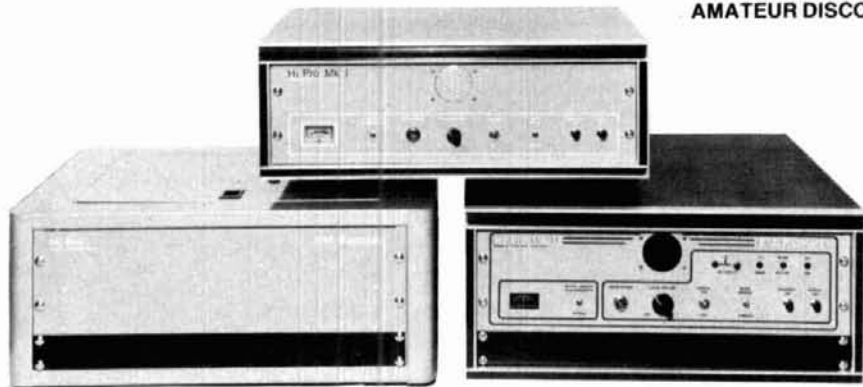
Hi PRO

VHF-UHF REPEATERS

SUPERIOR RECEIVER AND TRANSMITTER SPECIFICALLY DESIGNED FOR REPEATER SERVICE.

ADJUSTABLE TRANSMITTER POWER, FROM 1 TO 25 WATTS MINIMUM OUTPUT WITH EXTREMELY COOL OPERATION.—
AUTOMATIC BATTERY BACK UP SYSTEM CAPABILITY WITH BATTERY CHARGING AND REVERSE POLARITY PROTECTION.—
NOW WITH A FULL COMPLIMENT OF INDICATORS AND STATUS LIGHTS.—100% DUTY CYCLE—ADVANCED REPEATER SQUELCH
NO CHOPPING, POPPING, OR ANNOYING REPEATER KEY UPS DURING LIGHTNING STORMS.—DIE CAST ALUMINUM R.F.
ENCLOSURES —SMALL SIZE 5¼ x 19 x 13"—HIGH QUALITY LONG LIFE DESIGN.

AMATEUR DISCOUNTS AVAILABLE



Hi Pro

TRANSMITTER AND RECEIVER

USED IN ALL HI PRO REPEATERS

ASSEMBLED
SMALL SIZE
3½ x 6¼"



HI PRO TRANSMITTER
DESIGNED FOR REPEATER
SERVICE WITH EXCELLENT
AUDIO, STABILITY,
HARMONIC REJECTION
AND LOW NOISE

ADJUSTABLE
POWER
OUTPUT
UP TO 5 WATTS
FROM THE
EXCITER BOARD
COOL OPERATION

HI PRO RECEIVER
THIS RECEIVER IS THE
HEART OF THE REPEATER
AND BOASTS SUPERIOR
SQUELCH ACTION NEEDED
FOR THIS TYPE OF
SERVICE EXCELLENT
SENSITIVITY, STABILITY
AND SELECTIVITY

USE THIS RECEIVER
TO REPLACE THAT
TROUBLESOME RECEIVER
IN YOUR PRESENT
REPEATER



ASSEMBLED
SMALL SIZE
3½ x 6¼"

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THE HAM NOTEBOOK

Using macros with packet

Computers are supposed to reduce the drudgery of repetitive tasks. When operating packet, I get tired of using the keyboard to enter the same commands over and over. Such tasks can be automated and then invoked when needed by means of a computer programming technique called a "macro". According to the Lotus Development Corporation *Lotus 1-2-3 Reference Manual*:

"A macro performs a task automatically. To create a macro, you create a set of entries that describes a particular task keystroke by keystroke, and then name...[it]. To use a macro, you invoke it by pressing...the name of the macro."

If you'd like to tell your computer to send any of the following sample packet commands by using only two or three keys:

```
CONNECT W1JLI
CONNECT W1JLI-1
CONNECT W1KRU
CONNECT WB1GMA
BE 90
BT HELLO PACKET.. TOM, AD1B
CONVERS
```

A macro can handle any of these tasks easily. Even better, macros can be designed for your particular needs and utilized in many terminal programs.

I'm using an IBM PC for my packet

operations and have chosen the ProComm communications program for terminal emulation. ProComm lets you define up to ten different macros that can be invoked by holding down the ALT key and then pressing any number between 0 and 9. The command line that you have stored is typed on the screen; when you hit the RETURN key, the command is executed. Alternatively, you can include an "embedded" character in the macro so that a carriage return is sent when the macro is invoked.

Consider acquiring ProComm if you're using an IBM or compatible computer for packet or telecommunications. This "shareware" product is distributed by many clubs, bulletin boards, and software vendors at nominal cost. The only charge is a duplication fee which shouldn't exceed \$6. If you like the program and use it, you are asked to register your copy with the developers and pay the licensing fee (\$25) to: Datastorm Technologies, Inc., P.O. Box 1471, Columbia, Missouri 65205.

There are any number of commercial, shareware, and public domain programs that can be used to store combinations of keystrokes for later use. ProComm comes with an option to store up to ten different macros in the program itself. To access this option, you need only call the macro menu.

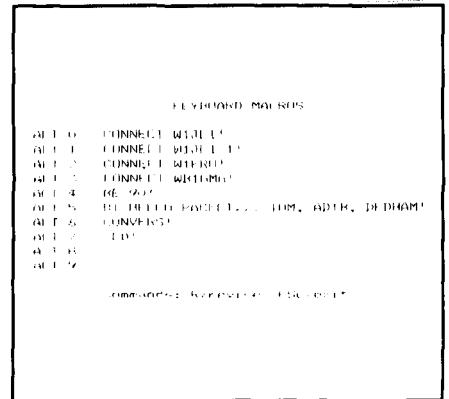
You can create and edit macros by holding down the ALT key and striking the "M" key (ALT-M). When you do this, a small menu appears that allows the definition of the ten available macro strings used as command lines.

Each macro is a string of up to 36 characters in length; it may contain embedded control codes (such as the CONTROL character) and carriage returns. You don't need to hit the RETURN key if you choose to use an embedded carriage return; it is sent automatically when you use the macro.

Figure 1 gives an example of the macro screen that is used to define or change a macro. It also contains samples of typical macros. The steps are simple:

- Call the macro menu with the ALT-M option.
- Type "R" to revise a macro.
- Strike a number (from 0 to 9) to select or name a macro.
- Enter the text string that you want to use.
- Respond with the letter "Y" to save the new macro.
- Revise another macro or hit the "ESCAPE" key to exit.

FIGURE 1



Macro screen.

Notice that all my macros end with an exclamation point. ProComm has a feature called Output String Translation — the program treats predefined characters in a special manner. The exclamation point is interpreted as a

carriage return; a caret ("^") is interpreted as the "control" character. If you want to send Control-C, include the "^C" string in your macro. Notice that macro number 7 in fig. 1 is the command "^CD!". This provides a Control-C (to call the command line on my terminal unit) and a D (for disconnect) followed by a carriage return. Macro number 7 is designed to disconnect and return to the command line.

Once the program is set up, you can use macros to speed up the entry of your ten most common terminal commands and execute them with only two keystrokes. If you forget the definition of any particular macro key, simply use the ALT-M combination to see the macro menu. I like macros; they provide an effortless way to get around that keyboard.

Thomas M. Hart, AD1B

Article 1 HAM RADIO

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<p>TRANSISTORS</p> <table border="1"> <tr><th>PART</th><th>TYPE</th><th>PRICE</th></tr> <tr><td>2N2222</td><td>NPN</td><td>10-42 5 for 75</td></tr> <tr><td>2N2904</td><td>PNP</td><td>10-5 3 for \$1.00</td></tr> <tr><td>2N2906</td><td>PNP</td><td>10-18 3 for \$1.00</td></tr> <tr><td>2N2907</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2908</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2909</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2910</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2911</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2912</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2913</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2914</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2915</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2916</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2917</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2918</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2919</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2920</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2921</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2922</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2923</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2924</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2925</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2926</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2927</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2928</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2929</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2930</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2931</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2932</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2933</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2934</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2935</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2936</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2937</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2938</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2939</td><td>PNP</td><td>10-42 5 for 75</td></tr> <tr><td>2N2940</td><td>PNP</td><td>10-42 5 for 75</td></tr> </table>	PART	TYPE	PRICE	2N2222	NPN	10-42 5 for 75	2N2904	PNP	10-5 3 for \$1.00	2N2906	PNP	10-18 3 for \$1.00	2N2907	PNP	10-42 5 for 75	2N2908	PNP	10-42 5 for 75	2N2909	PNP	10-42 5 for 75	2N2910	PNP	10-42 5 for 75	2N2911	PNP	10-42 5 for 75	2N2912	PNP	10-42 5 for 75	2N2913	PNP	10-42 5 for 75	2N2914	PNP	10-42 5 for 75	2N2915	PNP	10-42 5 for 75	2N2916	PNP	10-42 5 for 75	2N2917	PNP	10-42 5 for 75	2N2918	PNP	10-42 5 for 75	2N2919	PNP	10-42 5 for 75	2N2920	PNP	10-42 5 for 75	2N2921	PNP	10-42 5 for 75	2N2922	PNP	10-42 5 for 75	2N2923	PNP	10-42 5 for 75	2N2924	PNP	10-42 5 for 75	2N2925	PNP	10-42 5 for 75	2N2926	PNP	10-42 5 for 75	2N2927	PNP	10-42 5 for 75	2N2928	PNP	10-42 5 for 75	2N2929	PNP	10-42 5 for 75	2N2930	PNP	10-42 5 for 75	2N2931	PNP	10-42 5 for 75	2N2932	PNP	10-42 5 for 75	2N2933	PNP	10-42 5 for 75	2N2934	PNP	10-42 5 for 75	2N2935	PNP	10-42 5 for 75	2N2936	PNP	10-42 5 for 75	2N2937	PNP	10-42 5 for 75	2N2938	PNP	10-42 5 for 75	2N2939	PNP	10-42 5 for 75	2N2940	PNP	10-42 5 for 75	<p>10 AMP SOLID STATE RELAYS</p> <p>ELECTROLA S2181 CONTROL Rated 5.5 to 10 Vdc will operate on 3-32 Vdc LOAD 10 Amp @ 240 Vac 2 1/4" X 1 3/4" X 7/8" CAT# SSR1Y-10B \$9.50 each QUANTITY DISCOUNT 10 for \$85.00 25 for \$175.00 50 for \$300.00 100 for \$500.00</p>	<p>MINIATURE TOGGLE SWITCHES all rated 5 Amps</p> <p>S.P.D.T. (on-on) Solder lug terminals. CAT# MTS-4 \$1.00 each 10 for \$9.00</p> <p>S.P.D.T. (on-on) Non threaded bushing P.C. mount. CAT# MTS-40PC 75¢ each 10 for \$7.00</p> <p>D.P.D.T. (on-on) Solder lug terminals. CAT# MTS-8 \$2.00 each 10 for \$19.00</p>
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- ◆ Bit Inverted Baudot
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- ◆ ASCII High Speed
- ◆ ASCII Variable Speed
- ◆ Sitor Mode A (ARQ)
- ◆ Sitor Mode B (FEC)
- ◆ Autor
- ◆ ARQ 2&4 chan. (TDM)
- ◆ VFT Modes (FDM)
- ◆ Russian 3rd Shift Cyrillic
- ◆ Facsimile (FAX) AM
- ◆ Facsimile (FAX) FM
- ◆ Packet AX.25
- ◆ Literal Mode
- ◆ Databit Mode
- ◆ Diversity Reception
- ◆ Dual Metering
- ◆ Low Tone & High Tone
- ◆ Variable & Standard Shift
- ◆ Option: Real Time Clock
- ◆ Option: Video Display of Facsimile (FAX)
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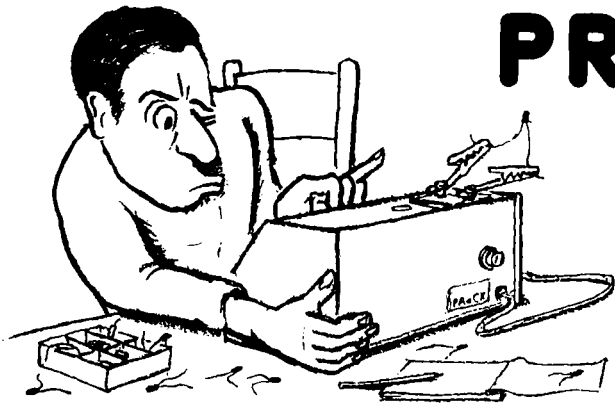
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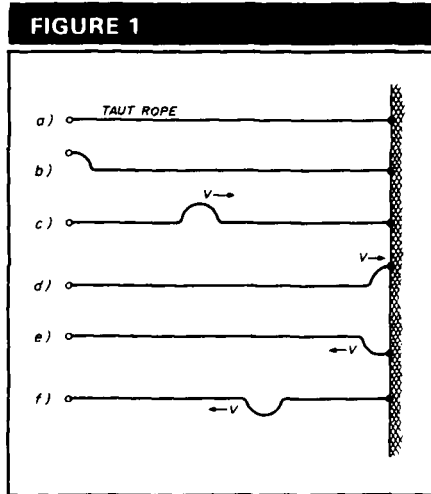
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Standing waves: a review

Standing waves are always a consideration when dealing with antennas, transmission lines, and other rf source/load combinations. This month I'll take a brief look at standing waves, how they're calculated, how they're measured, and what they mean.

The reflection phenomenon was mentioned in last month's discussion of the step function or single-pulse response of a transmission line; the same phenomenon applies when the transmission line is excited with an ac signal. Let's review what happens in a transmission line system under ac excitation by using a little metaphorical device — the old rope trick. In **fig. 1** a taut rope is anchored at one end to an inflexible wall (**1A**). If a pulse is initiated by wiggling the free end of the rope (**1B**), the displacement wave will propagate down the rope (**1C**) until it hits the wall (**1D**). At this point the wave is reflected (**1E**) and repropagates back down the rope toward the source (**1F**). In this case, there is a 180-degree phase reversal, but that only happens in some transmission line situations (in other cases the reflected



"Taut rope" metaphor for standing waves.

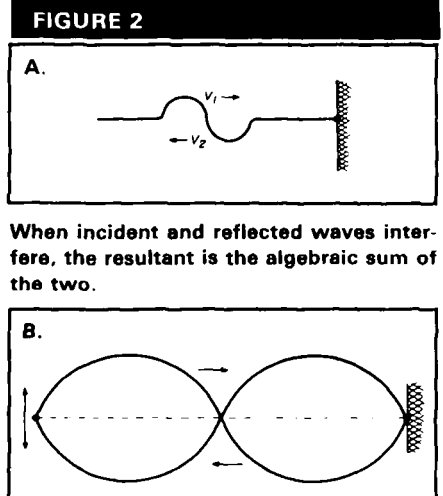
wave is in phase with the incident wave).

If the free end of the rope (our metaphorical "transmitter") is moved up and down, the rope oscillates and produces a series of waves. When an incident wave crosses a reflected wave the two will add algebraically as shown in **fig. 2A**. The amplitude at any given point is the sum of the two wave amplitudes; it may be either greater or less than the individual waves.

Figure 2B shows a situation in which the oscillations are recurrent in such a way that they produce standing waves on the rope. In this case, an

observer looking from the side would see what appears to be a single wave pattern standing in free space.

If a transmission line is perfectly matched to the load, no power is reflected back towards the source. This situation is analogous to a rope connected to a perfectly distensible foam rubber wall that absorbs all the mechanical energy of the rope wave. When a transmission line isn't matched to its load, some of the energy is absorbed by the load and some is reflected back down the line towards the source. This situation is



When incident and reflected waves interfere, the resultant is the algebraic sum of the two.

Oscillations on the input give rise to standing waves.

analogous to a rope connected to a somewhat distensible wall that absorbs some energy and reflects the rest. The interference of incident (forward) and reflected (reverse) waves creates standing waves on the transmission line.

The voltage or current measured along the line vary, depending on the load (see fig. 3). The voltage-vs.-length curve for a matched line is shown in fig. 3A, where $Z_L = Z_0$. The line is said to be "flat" because the voltage and current remain constant along the line. Figure 3B shows the voltage distribution over the length of the line when the load end of the line is shorted ($Z_L = 0$). At the load end the voltage is zero, a result of zero impedance. The same impedance and voltage situation is repeated every half wavelength down the line from the load end towards the generator. Voltage minima are called nodes, while voltage maxima are called antinodes.

The pattern in fig. 3C occurs when the line is not terminated (open); that is, Z_L is infinite. The pattern is the same shape as fig. 3B (shorted line), but phase shifted 90 degrees. In both cases the reflection is 100 percent, but the phase of the reflected wave is shifted 90 degrees.

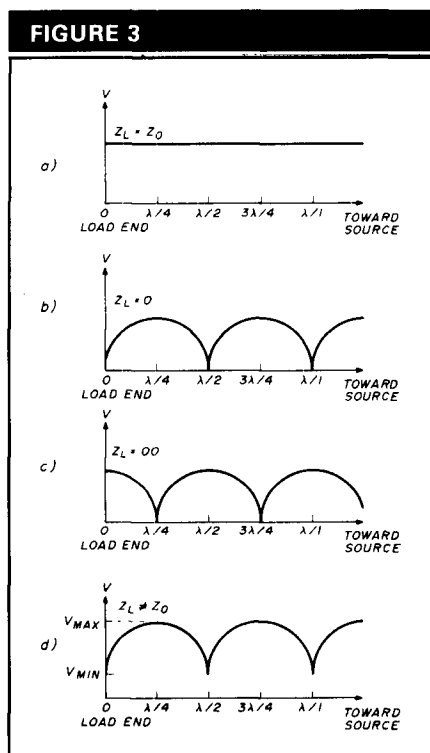
Figure 3D shows the situation where Z_L is not equal to Z_0 ; it is neither zero nor infinite. In this case the nodes represent some finite voltage, V_{min} , rather than zero. The standing wave ratio (SWR) reveals the relationship between load and line.

If the current along the line is measured, the pattern will resemble the patterns of fig. 3. The SWR is then called ISWR, to indicate that it came from a current measurement. It is called VSWR if the SWR is derived from voltage measurements. VSWR is the term most commonly used, perhaps because voltage is easier to measure.

VSWR can be specified in any of several equivalent ways:

From incident voltage (V_i) and reflected voltage (V_r):

$$VSWR = \frac{V_i + V_r}{V_i - V_r} \quad (1)$$



(A) Voltage vs. Length characteristic of transmission line: (a) flat line ($Z_L = Z_0$), (b) shorted line, (c) open line, (d) mismatched line.

From transmission line voltage measurements (fig. 3D):

$$VSWR = \frac{V_{max}}{V_{min}} \quad (2)$$

From load and line characteristic impedance:

$$(Z_L > Z_0) \quad VSWR = Z_L / Z_0 \quad (3)$$

$$(Z_L < Z_0) \quad VSWR = Z_0 / Z_L \quad (4)$$

From incident (P_i) and reflected (P_r) power:

$$VSWR = \frac{1 + [P_r/P_i]^{1/2}}{1 - [P_r/P_i]^{1/2}} \quad (5)$$

From reflection coefficient (p):

$$VSWR = \frac{1 + p}{1 - p} \quad (6)$$

It's also possible to determine the reflection coefficient (p) from knowledge of VSWR:

$$p = \frac{VSWR - 1}{VSWR + 1} \quad (7)$$

VSWR is usually expressed as a ratio. For example, when Z_L is 100

ohms and Z_0 is 50 ohms, the VSWR is $Z_L/Z_0 = 100 \text{ ohms}/50 \text{ ohms} = 2$, or VSWR = 2:1. VSWR can also be expressed in decibel form: $VSWR = 20 \log (VSWR)$

The SWR is important in systems for several reasons. At the root of it all is the fact that the reflected wave represents energy lost to the load. For example, in an antenna system less power is radiated if some of its input power is reflected back down the transmission line. This is because the antenna feedpoint impedance doesn't match the transmission line characteristic impedance. Now let's take a look at the problem of mismatch losses.

Mismatch (VSWR) losses

The power reflected from a mismatched load represents lost energy and, depending on the situation, will have implications that range from negligible to profound. A result might be anything from a slight loss of signal strength at a distant point from an antenna, to destruction of the output final amplifier device in a radio transmitter. The latter problem so plagued early solid-state transmitters that designers opted to include shutdown circuitry to sense high VSWR and limit output power proportionally.

VSWR on the transmission lines interconnecting devices under test, instruments, and signal sources can cause erroneous readings in radio system measurements, making them invalid. This problem is important, especially at VHF and with microwaves where transmission line lengths between signal sources, amplifiers, and indicating instruments are either an appreciable fraction of a wavelength or greater than a wavelength at those frequencies. For my MMIC column a few months back I built an amplifier that worked from near dc to 1 GHz or so. After making measurements above 400 MHz, I came up with a situation where there was more gain than the amplifier could offer. The "free" signal was actually wave combination in phase and *not* the gain of the MMIC amplifier.

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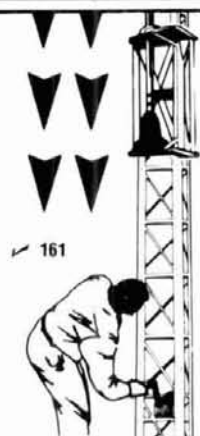
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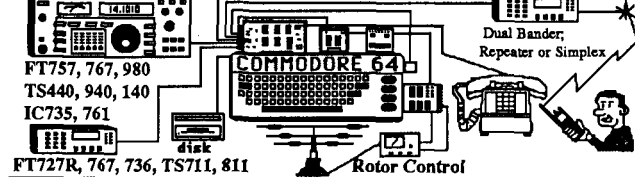
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You must take two VSWR situations into account when determining VSWR losses. Consider a transmission line of impedance Z_0 interconnecting a load impedance (Z_L) and a source with an output impedance (Z_s). There is a potential for impedance mismatch at both ends of the line.

Where one end of the line is matched (either $Z_s = Z_0$ or $Z_L = Z_0$), the mismatch loss due to SWR at the mismatched end is:

$$ML = -10 \log \left[1 - \left(\frac{SWR - 1}{SWR + 1} \right)^2 \right] \quad (8)$$

This can also be written as:
 $ML = -10 \log (1 - p^2)$

Example

A coaxial transmission line with a characteristic impedance of 50 ohms is connected to the 50-ohm output (Z_0) of a signal generator, and also to a 20-ohm load impedance (Z_L). Calculate the mismatch loss.

Solution:

First find the VSWR:

$$VSWR = Z_0/Z_L$$

$$VSWR = 50 \text{ ohms}/20 \text{ ohms} = 2.5:1$$

Mismatch loss:

$$ML = -10 \log \left[1 - \left(\frac{SWR - 1}{SWR + 1} \right)^2 \right] \quad (9)$$

$$ML = -10 \log \left[1 - \left(\frac{2.5 - 1}{2.5 + 1} \right)^2 \right]$$

$$ML = -10 \log \left[1 - \left(\frac{1.5}{3.5} \right)^2 \right]$$

$$ML = -10 \log [1 - (0.43)^2]$$

$$ML = -10 \log [1 - 0.185]$$

$$ML = -10 \log [0.815]$$

$$ML = (-10) (-0.089) = 0.89$$

When both ends of the line are mismatched a different equation is required:

$$ML = 20 \log [1 \pm (p_1 \times p_2)] \quad (10)$$

Where:

p_1 is the reflection coefficient at the source end of the line, $(VSWR_1 - 1)/(VSWR_1 + 1)$

p_2 is the reflection coefficient at the load end of the line, $(VSWR_2 - 1)/(VSWR_2 + 1)$

Note that the solution to eqn. 10 has two values: $[1 + (p_1 p_2)]$ and $[1 - (p_1 p_2)]$.

The preceding equations reflect the mismatch loss solution for low loss or "lossless" transmission lines. They are close approximations, but there are situations where they are insufficient — namely when the line is lossy. Though not very important at low frequencies, loss becomes significant at VHF through microwave frequencies. Interference between incident and reflected waves produces increased current at certain antinodes (which increases ohmic losses) and increased voltage at certain antinodes (which increases dielectric losses). The latter increases with frequency. Equation 11 relates reflection coefficient and line losses to determine total loss on a given line.

$$loss = 10 \log \left[\frac{n^2 - p^2}{n - np^2} \right] \quad (11)$$

Where:

loss is the total line loss in decibels

p is the reflection coefficient

n is the quantity $10^{(A/10)}$

A is the total attenuation in dBs presented by the line, when the line is properly matched ($Z_L = Z_0$)

Example

A 50-ohm transmission line is terminated in a 30-ohm resistive impedance. The line is rated at a loss of 3 dB/100 feet at 1 GHz. Calculate the loss in 5 feet of line, the reflection coefficient, and the total loss in a 5-foot line mismatched as above.

solution:

$$A = \frac{3dB}{100ft.} \times 5-ft = 0.15dB \quad (12)$$

$$p = \frac{Z_L - Z_0}{Z_L + Z_0} \quad (13)$$

$$p = \frac{50 - 30}{50 + 30}$$

$$p = 20/80 = 0.25$$

$$n = 10^{(A/10)}$$

$$n = 10^{(0.15/10)}$$

$$n = 10^{(0.015)} = 1.04$$

$$loss = 10 \log \left[\frac{n^2 - p^2}{n - np^2} \right] \quad (14)$$

$$loss = 10 \log \left[\frac{(1.04)^2 - (0.25)^2}{(1.04) - ((1.04)(0.25)^2)} \right]$$

$$loss = 10 \log \left[\frac{1.082 - 0.063}{(1.04) - ((1.04)(0.063))} \right]$$

$$loss = 10 \log \left[\frac{1.019}{1.04 - 0.066} \right]$$

$$loss = 10 \log \left[\frac{1.019}{0.974} \right]$$

$$loss = 10 \log (1.046)$$

$$loss = (10)(0.02) = 0.2dB$$

Compare the matched line loss ($A = 0.15$ dB) with the total loss ($loss = 0.2$ dB), which includes mismatch loss and line loss. The difference ($loss - A$) is only 0.05 dB. If the VSWR were considerably larger, the loss would rise. Work through some basic examples using VSWR values seen in Amateur Radio work; the answers may surprise you. Considering that an S unit is either 3 or 6 dB depending on which receiver you own, it isn't necessary to tweek out every little bit of VSWR. In fact, the only reasons to worry about it are that: the VSWR low point indicates resonance on the antenna, and solid-state final amplifiers are not too happy with VSWR.

Trimming the transmission line does not lower VSWR, despite what non-ideal instruments may lead you to believe. To reduce VSWR, you must either resonate the antenna or insert an impedance-matching device between the line and the antenna. The only time that transmission line can reduce VSWR is when it is used as a matching section, as discussed last month.

Editor's Note: This material was derived from Joe's forthcoming book, *Practical Antenna Handbook*. Joe Carr, K4IPV, can be reached at POB 1099, Falls Church, Virginia 22041; he'd like to have your comments and suggestions for this column.

Article J

HAM RADIO

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BOOK PAGE



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H. H. Beverage

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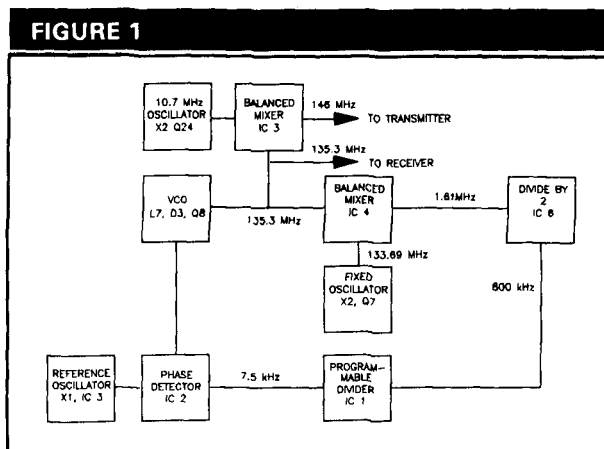
MORE FIXES FOR THE IC22S VHF RADIO

By Brian J. Henderson, VE6ZS, 23 Deermoss Place SE, Calgary, Alberta T2J 6P5 Canada

In its day, the Icom IC22S was one of the most popular radios sold. I still own two and have needed to repair them on a few occasions. One had a number of problems requiring major work. The radio's only shortcoming is that its manual gives little more than a circuit diagram; * I didn't find it particularly helpful. Some of the problems I've encountered and corrected are outlined here.

Theory and operation

A simplified block diagram is shown in fig. 1. A voltage-controlled oscillator (VCO) generates the frequencies required for the receiver and transmitter. The VCO operates at 135.3 MHz, the frequency required for receiver injection. The components used for phase detection and division won't operate at these high frequencies. The signal is mixed with a fixed frequency of 133.69 MHz generated by crystal X2 and Q7, which operate as a tripler. The difference between these two is 1.61 MHz. This signal is further divided by 2, by IC 6, and passed on to the programmable voltage divider, IC 1. The division of the signal by IC 1 is set by the diode matrix board and associated logic. The divided frequency is passed on to the phase comparator, IC 2. The frequency at this point should be about 7.5 kHz. Phase is compared with a reference 7.5-kHz signal produced by crystal X1 and fixed divider IC 3. The difference in phase and frequency between the fixed reference and the variable signal from the VCO is converted by IC 1 to a dc voltage (offset error voltage). The dc voltage is used to control the capacitance of D3 in the VCO. Changing the capacitance in the VCO will change its output frequency. The correction process continues until the VCO has the correct output frequency. This is achieved when the phase error between the reference and divided generated frequencies is reduced to zero. The PLL is then said to be "locked." When changing channels, or going from transmit to receive, repeat this process to give the required frequencies for the radio to operate.



Block diagram of the PLL in the IC22S.

Frequency alignment

Make adjustments in the following order using a frequency counter, signal generator, and a plastic tuning tool.

• Reference Oscillator

Connect the counter to test point CP1 on the PLL board (located on the lower left corner of the PLL board). Adjust C2 for a frequency of 7.68 MHz (European version 10.24 MHz).

• Receive Frequency

Using a signal generator, inject a signal on a channel the radio can receive. The wire originally connected to pin 1 of the accessory socket is the discriminator output. Adjust C38 on the PLL board (lower left corner of board next to crystal X2) for zero discriminator current as measured between this point and chassis ground.

• Transmit Frequency

Most radios are usually on frequency and require no adjustment; should yours need it, transmit on a known frequency. If the radio is off frequency, as displayed on the counter, adjust L41 (located at the front, near the left corner of the main board) for the correct transmit frequency.

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CT-125	10 Hz-1.25 GHz	<25mV @ 50 MHz <15mV @ 500 MHz <100mV @ 800 MHz	1 PPM	9	0.1Hz, 1Hz, 10Hz	189.95
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VCO adjustment

I've had several problems with cold weather and PLL lockup. No specifications were given in the manual. Set the radio to 147 MHz (or the center of your desired operating range). Monitor the voltage between pin 1 of IC 2 and ground. Adjust L7 (inside the VCO can) for a voltage of 3.5 volts. This won't affect the frequency of operation if the radio has been adjusted according to the previous steps. Note that the radio's maximum operating bandwidth is approximately 2.5 MHz. Bear this in mind when choosing the center frequency.

PLL board jumpers

I traced a number of intermittent PLL lockup problems to the jumpers connecting the top and bottom of the PLL board. The original board didn't use plated-through holes, and these jumpers connected the top and bottom. Stainless steel wire was used originally; it doesn't solder well. Remove all these jumpers and replace them with tinned copper wiring. There are about 20 jumpers to replace.

PLL logic

The radio will work in simplex mode below 146 MHz if the VCO is adjusted as I explained above. However, the logic won't add the correct offset for the 600-kHz shift normally required if it's in the duplex mode. I added IC 11 (two gates) to correct this design problem. The gates can be installed by cutting traces, but I've had numerous problems with broken circuit traces on the PLL board. I removed all four existing ICs of the logic circuit (ICs 7, 8, 9, and 10) and built an entirely new logic board. I used wire-wrap techniques to construct the board and mounted it with L-brackets. The L-brackets attach to the sides of the chassis towards the rear, underneath the normal position of the speaker. Be sure to leave a 1-inch (2.5 cm) space between IC 7 and 8, and IC 9 and 10 for the speaker coil. I found that the wire-wrap pins were too long and interfered with the solder side of the main board when mounting this extra board. I cut off the excess pins so there was sufficient clearance for mounting.

Wire the extra board to the diode matrix board plug-in connection block on the PLL board. Resistors R36 and R37 are shown in fig. 2. These resistors are already installed in the radio. You don't have to add them if the input wiring to the logic board (D0-D7) is wired directly to the diode matrix board plug.

Wiring out of the logic board (D0-D2, P3-P7) connects to the input pins of the programmable divider (IC 1). These connections are shown on the original schematic. D0, D1, and D2 don't go through the logic board. They connect directly to pins 1, 2, and 3 of the programmable divider.

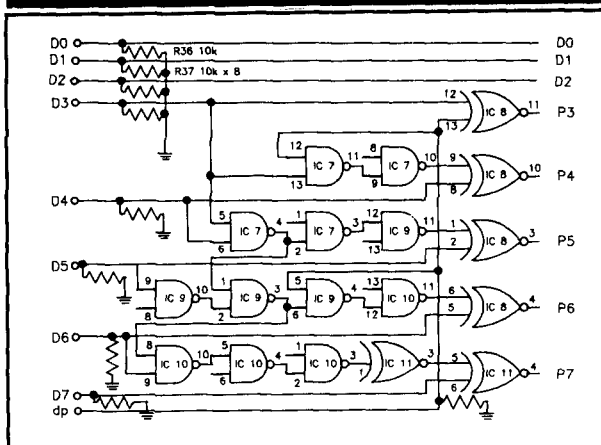
Common 4000 or 14000 series chips can be used as direct replacements for ICs 7, 8, 9, and 10 if removed or damaged. After installing this extra circuit board, I've had virtually no further intermittent problems with the PLL board.

Microphonics

One of the largest problems with frequency synthesizers is the mechanical vibration of the components in the synthesizer. This vibration can be heard as audio on an FM transmitter. It can also be heard in the speaker as an "echo" or hollow sound during receive. These vibrations are called "microphonics" and can result from speaker or microphone audio being coupled to the synthesizer. This means that everything inside the VCO must be "glued" together so it won't move mechanically.

There is a resin or hard material inside the VCO shielded box holding everything together so that it won't vibrate. If you remove it, you must replace it for the radio to operate without these microphonics. Beeswax is the easiest material to use. It's chemically inert and melts at

FIGURE 2



Schematic of the duplex offset logic board showing the addition of IC 11.

temperatures low enough that it will not damage components. You can find beeswax in sewing and fabric stores.

The beeswax can be melted in a small container, poured in, and allowed to set. Don't fill the VCO can completely — just enough to cover the components and keep them from vibrating. If it becomes necessary to remove the beeswax for further servicing, remove the VCO can and heat with a candle. The beeswax will melt and run out.

Component substitution

The original components can usually be replaced with substitutes from any cross-reference book. One com-

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ponent I found particularly difficult to replace was the varactor diode in the PLL circuit. Cross-referencing the original part was next to impossible. By trial and error and some calculations, I determined that the diode I needed was a 1N5441A, MV 2101, or ECG610 varactor diode.

Circuit board cleaning

It appeared that the flux from component soldering was never removed when the board was manufactured. Flux is quite corrosive and will eventually eat its way through a circuit board. Remove as much of it as you can with flux remover, available at most electronics stores.

Nine-volt supplies

There are three 9-volt regulated power supplies in the radio: one common, one for transmit, and one for receive. Each 9-volt regulator transistor has a 15-ohm resistor in series with the collector. This resistor was originally installed with a power rating of 1/4 watt. I recommended that you change R141, R144, and R149 to a 1-watt rating, as the original components run too hot.

Transmitter tuning

Six trimmer capacitors are involved in aligning the transmitter. Set the radio to a frequency below the midpoint of the desired operating range — for example, 146.5 MHz if the center of the operating range is 147 MHz. Adjust C97, C100, C92, C91, C85, and C81 in that order for maximum power output into a matched load. Repeat these adjustments at least once.

Other adjustments

Here are some other common adjustments inside the radio:

- Deviation — R112 — located near the front center of the main board
- Low Power — R149 — located to the right of R112
- Mic Gain — R132 — located near the front of the main board near the right side
- Power Meter — R73 — located near the back of the radio in the shielded can
- S-meter — R23 — located near the front center of the main board

Conclusion

I've gained a lot of experience over the years from servicing a number of these radios. A service manual is unavailable, and the owner's manual contains little information pertaining to serviceability. These changes and notes should help you fix some of the minor problems which can occur in an older radio.

*Icom USA verifies that no service manuals were printed for the IC22S. Schematics can be provided by Icom upon request. Ed.

Article K

HAM RADIO

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by Bill Clarke WA4BLC

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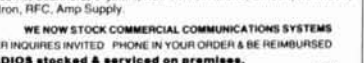
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DX FORECASTER

Garth Stonehocker, KØRYW

High sunspot propagation problems: part 2

Events that originate with solar flares cause propagation problems for Dxers and ragchewers alike. A sequence of events happens after a flare. Some (like sudden ionospheric disturbance, SID) occur shortly after the flare, some (like polar cap absorption, PCA) appear several hours later, and the final event (fade out) occurs from 1 to 3 days following the flare. The first two situations and remedies for them were discussed last month. These events will occur more frequently with the increased probability of large flares as the 11-year solar cycle reaches higher sunspot numbers and solar flux; be prepared with a remedy.

Fade out

Fade out is the most complicated and encompassing of all the ionospheric disturbances. It can affect propagation paths during the day or night, but the effect is worse at night. It lasts at least a day or two and is generally worldwide in extent, although the effects and severity differ with latitude and longitude. Fade out

is initially caused by the electrons that were ejected outward by the sun's flaring. These electrons are usually lower in energy than protons so they don't have the proton's speed, but they are more numerous. Being charged particles, the electrons are constrained to follow the solar magnetic field as they leave the sun. They travel with the solar wind, increasing its number density greatly and its speed a little. Those coming close enough to the earth's magnetic field veer into the polar regions along those magnetic field lines. Most of the electrons are high and weak enough to be fed into the geomagnetic field tail, captured, and then released at lower latitude into the ionospheric F region at night. It takes electrons some 1 to 3 days after the flare to affect the ionosphere due to their lower energy, the long solar path, and the delay caused by the earth's capturing some to release at night.

The latitude ion density distribution in the F region is normally at its highest in the equatorial latitudes from 30 degrees south to 30 degrees north. This is because the lower regions (D and E) are where the largest production of latitude ions from sunlight exists. When these ions drift to the F region up the field lines, the maximum density changes from its position along the geographic equator to one along the geomagnetic equator. The other ionospheric production region comes from the polar particles. Moving slightly toward the equator from the auroral zone (an area of no production) you'll find the F region trough, particularly on winter nights. However, when the electrons start coming

"hard" into the E region or "soft" from the tail into the F region, the trough widens and moves down even more toward the equator. How does this affect propagation and DX? The propagation paths at midlatitudes in east-west directions, like the United States to Europe or the Orient, go across higher latitudes. When the particles arrive, the auroral oval and trough come down right across your path, and the fade out has hit. Two things happen: the increase in the number of particles weakens the signal trying to get through, and the trough's lower density causes a decrease in maximum usable frequency (MUF). These decreases are not smooth, but variable (in seconds/minutes), and fluctuate over the 2 or 3 day period. The one difference between SID and fade out is that SID has a smoother decrease. The K figure broadcast at 18 minutes after the hour over radio station WWV is a measure of the geomagnetic-field ionosphere variations compared to the normal 3 hours of the day. It can be used to calibrate a path during non-disturbed periods which is used, in turn, to forecast how bad the propagation is when a fade out occurs. Fade outs from flares are more intense but of shorter duration than those from thin coronal solar wind increases.

The weak, variable signal strength and decreased MUF are hard to remedy. Ordinarily, the weak signal remedy for absorption is to increase the operating frequency as you would in the SID's remedy. But here MUF is decreasing on the propagation path, which calls for decreased operating

GMRT	0000	0100	0200	0300	0400	0500	0600	0700	0800	0900	1000	1100	1200	1300	1400	1500	1600	1700	1800	1900	2000	2100	2200	2300
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OCTOBER

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	N	NE	E	SE	S	SW	W	NW	PDT	5:00	6:00	7:00	8:00	9:00	10:00	11:00	12:00	1:00	2:00	3:00	4:00	5:00		
ASIA FAR EAST	20	30	20	10	12*	12	10	15	20	20	30	40	40	30	40	40	30	30	40	40	30	40	40	20
EUROPE	30	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
S. AFRICA	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
S. AMERICA	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
ANTARCTICA	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
NEW ZEALAND	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
OCEANIA AUSTRALIA	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
JAPAN	20	40	20	15	15	12	15	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40

Region	MID USA																							
	N	NE	E	SE	S	SW	W	NW	MIDT	6:00	7:00	8:00	9:00	10:00	11:00	12:00	1:00	2:00	3:00	4:00	5:00	6:00	7:00	
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Region	EASTERN USA																							
	N	NE	E	SE	S	SW	W	NW	EDT	8:00	9:00	10:00	11:00	12:00	1:00	2:00	3:00	4:00	5:00	6:00	7:00	8:00	9:00	
ASIA FAR EAST	30	40	20	12	12	12	12	20	30	30	40	40	30	40	40	30	30	40	40	30	40	40	30	40
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 *Look at next higher band for possible openings.

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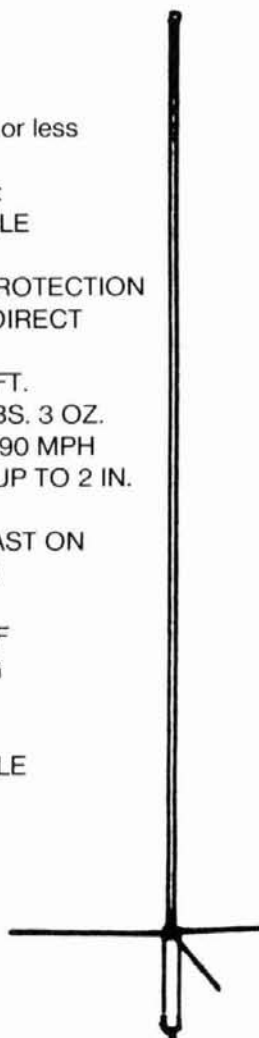
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frequency. You can try a combination of the two to determine which part of the problem is worse and go from there, or try VHF frequencies that may be getting through on auroral scatter. An alternate route south of the usual beam bearing (called side scatter at hf) may work, or long-path propagation may exist.

Last-minute forecast

The lower bands, 30 to 160 meters, are expected to be best the first and third weeks of October due to a dip in solar flux. Lower thunderstorm noise and summer absorption in the Northern Hemisphere will make a noticeable improvement in these bands. Expect some fade out to affect propagation during this equinox season around the 6th, 16th, 22nd, and 28th. The higher DX bands should improve the second week and be best the third week, as the result of a solar flux increase. Watch out for flare effects, SID, and PCAs during this activity. The Orionids meteor shower will be visible from the 15th to 24th of October, with a maximum rate of between 10 to 20 per hour on the 20th to 21st of the month. The moon is full on the 25th and perigee occurs on the 23rd.

Band-by-band summary

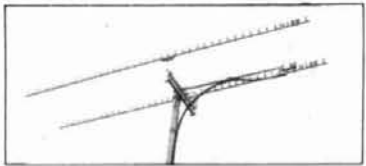
Ten, 12, 15, and 20 meters will provide many openings during the day. As you go up in frequency the openings will be shorter, centered around noon, and mainly towards the south. Twenty meters, the mainstay daytime band for northerly directions, will be useful towards the south in the evenings. Transequatorial openings might occur in the evening hours to southern locations if antenna radiation angles are down to 10 degrees.

Thirty, 40, 80, and 160 meters are all good for nighttime DX. Thirty and 40 meters are the night frequencies for the east, west, and northerly directions, and for distances of 1600 miles. Try 80 and 160 if disturbed conditions exist. These bands should be getting quiet, if fall weather frontal thunderstorms are absent.

Article L

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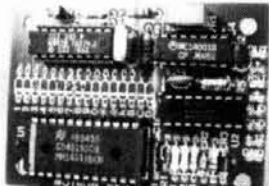
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

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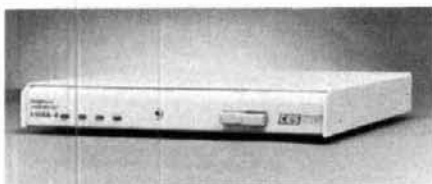
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Other features include: multi-digit DTMF connect code, activity timers, time out timers, CW ID, toll restrict and disconnect override code — all programmable by use of any DTMF telephone with a special security access code. In addition, remote base station operation is enabled by special security code, repeater logic control is provided for making a repeater with autopatch capability out of two transceivers, and the unit is reverse-patch capable with automatic ringout upon receipt of an inbound call.

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The Voice Box uses a 32-kHz sampling rate and several filters for high-quality audio. It automatically keys the PTT line to your transmitter or transceiver during playback, and also allows

(continued on page 105)

CELEBRATE

the 75th anniversary of ARRL with a new Handbook!

1989 marks the 75th anniversary of the founding of the League. There's no better way of celebrating this momentous occasion, than with the new *1989 ARRL Handbook for the Radio Amateur!*

The 1200-page sixty-sixth edition contains over 2100 tables, figures and charts. The new *Handbook* is better than ever with revised information on phase noise measurement, direct frequency synthesis and spread spectrum communication techniques. The section on repeaters has been updated including a new CW identifier circuit. You'll find new spectrum analyzer and oscilloscope material, as well as several new projects in the test equipment chapter.

As always, we've added a host of new construction projects to this new edition. Just some of the new projects include: A 500-MHz frequency counter, 160 through 10 meter legal limit amplifier, simple CMOS keyer project, digital audio memory keyer and a L/Q meter for measuring coil inductance.

But that's not all. You'll find many other popular construction projects that can be built in a weekend such as power supplies and VHF/UHF preamps. For the more ambitious builder there are projects like the 1.8 MHz QSK transverter (there are VHF/UHF transverter projects too) and there are many amplifier designs to suit your needs from HF through microwaves.

The Handbook has always been famous as a reference for component data and you will find an entire chapter devoted to everything from transmitting tube and transistor specifications to aluminum tubing sizes. Satellite enthusiasts will find that the digital TR sequencer will add operating convenience to your station. Of course, you'll find the most up-to-date information on digital techniques, and the *video communications chapter* is packed with information not only on SSTV, ATV and FAX but Weather FAX as well. QRP enthusiasts will find the famous "Cubic incher" transmitter; not much bigger are the QRP SWR indicator and QRP Transmatch. There is also a VXO-controlled 6-watt CW transmitter for your favorite band between 80 and 15 meters. There are a number of useful station accessories that you can build like DTMF encoders and decoders, PIN-diode TR switch, digital PEP wattmeter and SWR calculator, Transmatches and dummy loads.

For \$21, *The ARRL 1989 Handbook for the Radio Amateur*, remains an exceptional value for a hardcover technical publication. The price outside the US is \$23. For postage and handling, add \$2.00 (or \$3.50 for insured mail or UPS — please specify)



Here is a description of what is covered in the Handbook:

The first 5 chapters serve as an introduction and cover: basics of Amateur Radio, electrical fundamentals, radio design technique and language, and solid state fundamentals. Vacuum tube principles as they pertain primarily to high power amplifier design are also presented in these introductory chapters. There are 12 chapters devoted primarily to these radio principles: power supplies, audio and video, digital basics, modulation and demodulation RF transmitters, receivers, transceivers, repeaters, power amplifiers, transmission lines and antenna fundamentals. Another 4 chapters cover voice, digital, image and special modulation techniques. The RF spectrum, propagation and space communications are covered in 2 chapters. The construction and maintenance section has 12 chapters of useful projects ranging from power supplies and antennas through digital equipment. You'll find up-to-date component data that the Handbook is famous for. The final 5 chapters cover how to obtain your license, station design and operation, interference, monitoring and direction finding. An *abbreviations list*, *huge index* and *etching patterns* make up the balance of the book.

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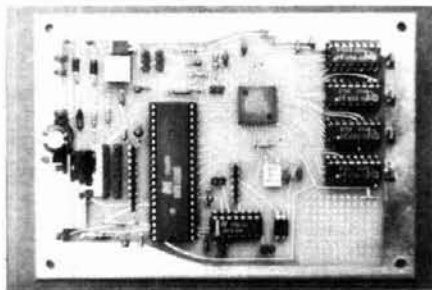
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(continued from page 102)



normal VOX operation. It has a switchable built-in microphone preamp to accommodate a wide variety of microphones and the audio output level to the transmitter is continuously adjustable. The Voice Box can be powered from a 10 to 16-Vdc source.

The Mini Voice Box has all the features of the regular Voice Box except that it has one voice message channel with up to 8 seconds of message time.

The Voice Box and the Mini Voice Box are shipped in kit form only. The kits consist of assembled, tested, working boards with complete instructions for installing the board in a suitable enclosure. Some standard offboard components (pushbuttons, toggle switches, microphone and power connectors, etc.) are required to complete the unit. They are available as an option.

Due to the current RAM shortage, Voice Box boards are being shipped without memory. Four plug-in 41256 (any speed) RAM chips are required to make the Voice Box operational. (The Mini Voice Box takes one.)

The introductory price of the Voice Box kit is \$95. The Mini Voice Box kit price is \$55. The off-board components option runs \$20 for the Voice Box and \$10 for the Mini Voice Box. To order send check, money order, or C.O.D. to QRZ Industries, P.O. Box 160, Piedmont, South Carolina 29673. Add \$10 for shipping and handling, and \$5 for C.O.D. orders. South Carolina residents add 5 percent sales tax. Please state name of publication where seen when placing order or requesting information.

Circle #313 on Reader Service Card.

Computerized DXing with software for IBM PC/XT/AT

The new MFJ-1286 Gray Line DX Advantage/Terminator is a computerized DXing tool

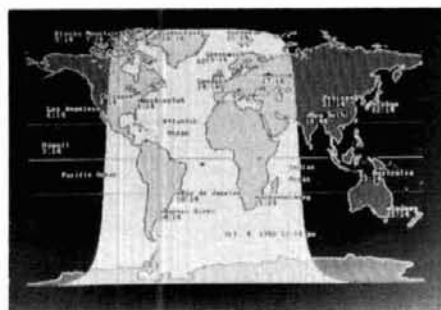
that predicts DX propagation by giving users instant access to Gray Line positions for any place in the world, at any time and date from 1980 to 1999.

You get a high resolution world map that displays the Gray Line as a moving area of day and night which changes with time. It shows you the moving Gray Line, UTC times, time zones, sun position over the earth, and latitude/longitude markers.

You can customize the MFJ-1286 Gray Line DX Advantage and display time and location for any QTH in the world. Run it by itself or as a memory resident program, in conjunction with your beam header or other software. It works with all graphics: Hercules, CGA, EGA and composite.

It comes with three maps: a default Land Mass Map, a map that shows the latitude/longitude markers, and a third map that displays the division of time zones throughout the world. CGA works with the Landmass Map and lets you send the display to your printer.

It also corrects for the north/south position of the sun and the curvature of the earth, making it perhaps the most accurate Gray Line predictor yet.



Pressing a function key switches the new MFJ-1286 Gray Line DX Advantage to a high speed display mode. This lets you watch solar and Gray line positions change in increments of 2 minutes, 6 minutes, 1 hour, 1 day, or 1 week. You can also pause the high speed display to study a position.

The MFJ-1286 retails for \$29.95 and is available from any MFJ dealer or direct from MFJ Enterprises Inc.

For more information contact MFJ Enterprises, Inc., P.O. Box 494, Mississippi State, Mississippi 39762.

Circle #314 on Reader Service Card.

Universal M-7000: new communications terminal

Universal Shortwave offers an exciting new product — the Universal M-7000 military-grade communications terminal. This self-contained device connects to the audio output of any quality communications receiver. Output is to a video

(continued on page 106)

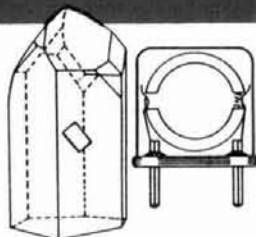
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(continued from page 105)

monitor (serial and parallel printer ports are also provided). The M-7000 decodes and displays all standard transmission modes: Morse code; Baudot, ASCII, Packet and Sitor A and B. Less common modes such as bit-inverted Baudot, high speed ASCII, ARQ-Moore (TDM), and Frequency Division Multiplex (FDM-VFT) are also supported. Other special display modes include Russian Third Shift Cyrillic, Literal, and Databit mode. The M-7000 also prints high quality facsimile (FAX) images to the parallel printer port.

Microprocessor controlled, switched capacitor filters comprise the prefilters, the channel filters, and the post detection low pass filter.

The M-7000 offers advanced monitoring features including: diversity inputs, split screen ARQ, remote terminal control, speed readout, screen saver, screen print, ten memories, Sel-Cals, auto-start, and screen print. Automatic filter tuning and auto-tune features provide semi-automated operation for maximum convenience.



The M-7000 is manufactured in Englewood, Florida by Digital Electronic Systems. Available factory installed options include a Real Time Clock and a Video FAX option. The M-7000 is available from stock at Universal and other selected dealers.

For additional information contact Universal Shortwave Radio, 1280 Aida Drive, Reynoldsburg, Ohio 43068.

Circle #315 on Reader Service Card.

New personal-scanning receiver offers 100 channels and all-band coverage

AOR, Ltd. has introduced of a new 100-channel hand-held receiver that offers complete public service band coverage.

The new radio measures 5-3/4" x 2-1/8" x 1-3/4". The receiver's frequency coverage is: 27-54 MHz, 108-174 MHz, 406-512 MHz, and 830-950 MHz. This allows coverage of all the police, fire and emergency bands, plus the new services now available above 800 MHz in 12.5, 25, and 30 kHz increments.



At 12 ounces total weight the model AR900 can be carried in a pocket, with the standard belt clip, or in an optional leather carry case.

Twenty-five front panel keys allow programming of five banks of 20 channels. Pairs of upper and lower limits for bands to be searched can be stored in 5 separate search memory locations. Information is stored in three permanent memories, which never lose program information should the batteries be disconnected. Extra features include first channel priority, keyboard lock-out, BNC antenna connector, and a blue-green display backlight for night use. The LCD display offers 22 separate prompting annunciators.

The suggested retail price is \$299. This includes a 450 MAH rechargeable battery, ac charger/adaptor, two antennas, and a stainless steel belt clip.

For further information contact ACE Communications, Monitor Division, 10707 East 106th Street, Indianapolis, Indiana 46256.

Circle #316 on Reader Service Card.

CS64W Connect-A-Call Telephone repeater

Engineering Consulting's "Connect-A-Call" (a telephone repeater) that is a cartridge for the Commodore (C-64, C-64C, C-128) computer. The cartridge works in three modes.

Mode #1 allows access to your Watts line from any phone — including cellular. It has multi-user options with multiple access codes and a logging option to provide usage time, and number dialed.

Mode #2 connects incoming calls to other telephone numbers if there is no answer after a preset number of rings. It can be remotely reprogrammed to change message, ring count, access codes, and delays.

Mode #3 re-directs incoming calls manually or automatically via access code, to as many as 1000 numbers.

The telephone repeater is dual amplified, and is powered by the computer. Connect-A-Call is available for \$399.95 from Engineering Consulting, 583 Candlewood St. Brea, CA 92621

New database provides high-speed device selection

Motorola has introduced the Motorola Data Disk: Discrete Semiconductor Version. This IBM PC-compatible (384K RAM required) high-performance database permits rapid automated search and selection of Motorola's entire discrete semiconductor portfolio. The high-density selector guide contains 58 product categories with technical information for over 7,200 devices, 20,000 cross references, over 200 standard package types, and 130,000 parameters. It supports both part number and parametric searches.

The Discrete Data Disk provides Sales Office and Distributor information for hundreds of Motorola worldwide locations, support for five languages, user color support (including monochrome), a printer utility, help screens, an information request form, and "smart" message lines. The disk also includes toggles allowing selection across surface mount devices only, military devices only, or surface mount military devices only. The message lines use the "progressive disclosure" technique eliminating the need for a user's manual.



Within the next year, the capabilities of the Data Disk will be expanded to include parametric information for all 30,000-plus Motorola Semiconductor products (ICs as well as Discretes), complete with cross references and prices.

Copies of the Motorola Discrete Semiconductor Data Disk are available for \$2.00 each by requesting DK101/D REV 1 from the Motorola Semiconductor Literature Distribution Center, P.O. Box 20912 Phoenix, Arizona 85036. The Data Disk is also available to Motorola customers through their local Motorola Semiconductor Sales Offices.

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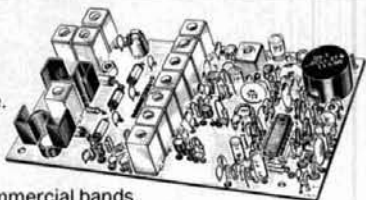
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Self-sufficient equations use no intermediate steps

The versatile Pi network couples transmitter output stages to antennas while acting not only as a transformer, but as a filter and antenna tuner. It is a "conjugate impedance" network.¹ The first step for determining the network frequency response and the limits of the antenna tuning range (for either analysis or design) requires equations for each of the reactive elements. There are many articles on Pi networks with various procedures for determining the required network reactances.²⁻⁷ Two new equations presented here for the shunt capacitors are self-sufficient and use no intermediate steps or square root factors.

Pi network circuit

Figure 1 is an apparatus diagram for a Pi network. It shows the terminations and reactive elements, with definitions for the resonant frequency impedances of each. Figure 2 shows these impedances in a circuit with a resistive match to the transmitter and load resistances. Definitions are included for capacitor element Q's and the "operating Q" to aid in circuit analysis.

There are three reactive elements, a series inductor and two shunt capacitors. As stated above, the circuit is a conjugate impedance network. At the resonant frequency, the resistive transmitter output stage and the equivalent parallel resistance of the antenna load are exactly matched by the network's terminal impedance, as shown in fig. 1.

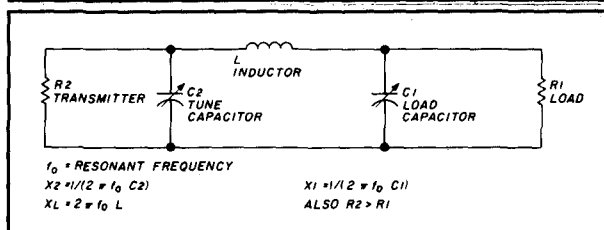
The application of the conjugate impedance condition to the general circuit equations results in the development of a fourth factor, the operating Q. Choosing this

gives you a measure of control over the design. Q_{3dB} is always less than one-half of Q_0 . Equations relating the above four factors are the subject of this article. Their derivation is given in the appendix.

The three equations

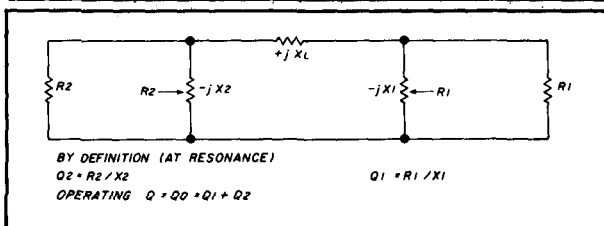
There are three equations, two of them new. The known equation^{2,3} contains the dependency between Q_0 and the inductive reactance X_L . This third equation can be arranged as a solution for either Q_0 or X_L ; each depends on the other. Given Q_0 , there is only one inductive reactance X_L that goes with it, and vice versa. It should be obvious which of the two arrangements to use. The known equation plus the two others complete the set of equations to be calculated.

FIGURE 1



Pi-network apparatus diagram.

FIGURE 2



Pi-network circuit schematic.

First choose either Q_0 or X_L ; then calculate the other. If X_L is given:

$$Q_0 = \frac{(R_1 + R_2) + 2\sqrt{R_1 R_2 - X_L^2}}{X_L} \quad (1)$$

If Q_0 is given:

$$X_L = \frac{Q_0(R_1 + R_2) + 2\sqrt{R_1 R_2} \sqrt{Q_0^2 - (R_2 - R_1)^2}}{Q_0^2 + 4} \quad (2)$$

With Q_0 and X_L established, the two new symmetrical capacitor equations are:

Load:

$$X_1 = \frac{2R_1}{Q_0 - \frac{(R_2 - R_1)}{X_L}} \quad (3)$$

Tune:

$$X_2 = \frac{2R_2}{Q_0 + \frac{(R_2 - R_1)}{X_L}} \quad (4)$$

With nominal conditions, Q_0 would be chosen somewhere between 10 and 20. This calls for the use of eqn. 2 to determine the associated inductive reactance X_L . The load capacitor X_1 and the tune capacitor X_2 follow.

For another circuit (some other load condition, for instance) X_L is now fixed and you'll need to determine the changed Q_0 . Equation 1 is indicated in this situation.

For either circumstance, with a paired Q_0 and X_L defined, eqns. 3 and 4 directly determine X_1 and X_2 for the two capacitors.

For example, assume the transmitter R_2 is 5000 ohms, the antenna 50 ohms, and that a Q_0 of 15 has been chosen. Then:

$$\begin{aligned} Q_0 &= 15 \\ X_L &= 379.99 \text{ ohms} \\ X_1 &= 50.67 \text{ ohms} \\ X_2 &= 356.80 \text{ ohms} \end{aligned}$$

Suppose that the load R_1 is changed to 100 ohms with a SWR of 2, and that X_L just determined is fixed. Then:

$$\begin{aligned} X_L &= 379.99 \text{ ohms} \\ Q_0 &= 16.56 \\ X_1 &= 54.57 \text{ ohms} \\ X_2 &= 339.50 \text{ ohms} \end{aligned}$$

There is only about a 6-percent change in the calculated factors when the load is resistive; for reactive loads the change is greater.²

Appendix

Derivation of the new equations for the two capacitors in the Pi network begins with two known equations^{2,8}. These equations have the disadvantage of using square roots:

$$X_1 = \frac{R_1 X_L}{R_1 + \sqrt{R_1 R_2 - X_L^2}} \quad (5)$$

$$X_2 = \frac{R_2 X_L}{R_2 + \sqrt{R_1 R_2 - X_L^2}} \quad (6)$$

Divide both sides of eqn. 5 by R_1 and both sides of eqn. 6 by R_2 . Invert both and use the definition of Q_1 and Q_2 to obtain:

$$Q_1 = \frac{R_1 + \sqrt{R_1 R_2 - X_L^2}}{X_L} \quad (7)$$

$$Q_2 = \frac{R_2 + \sqrt{R_1 R_2 - X_L^2}}{X_L} \quad (8)$$

The sum of eqns. 7 and 8 is Q_0 , agreeing with eqn. 1 given earlier. The difference is the compact equation:

$$Q_2 - Q_1 = \frac{R_2 - R_1}{X_L} \quad (9)$$

Adding and subtracting this to the equation $Q_0 = Q_1 + Q_2$ gives:

$$Q_1 = \frac{1}{2} \left(Q_0 - \frac{R_2 - R_1}{X_L} \right) \quad (10)$$

$$Q_2 = \frac{1}{2} \left(Q_0 + \frac{R_2 - R_1}{X_L} \right) \quad (11)$$

Finally, inserting the definitions of Q_1 and Q_2 in terms of their impedances, the capacitive reactances at the resonant frequency are:

Load:

$$X_1 = \frac{2R_1}{Q_0 - \frac{R_2 - R_1}{X_L}} \quad (12)$$

Tune:

$$X_2 = \frac{2R_2}{Q_0 + \frac{R_2 - R_1}{X_L}} \quad (13)$$

completing the derivation of the new pair of equations.

references

1. Walt Maxwell, W2DU, "Technical Correspondence", *QST*, March 1985, page 45.
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3. Elmer A. Wingfield, W5FD, "New and Improved Formulas for the Design of Pi and Pi-L Networks," *QST*, August 1983, page 23.
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5. William Orr, W6SAI, *Radio Handbook*, 22nd edition, Howard W. Sams, 1981, page 11-33.
6. ARRL *Radio Amateur Handbook*, 1984, page 2-48 and 2-49.
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Article M

HAM RADIO



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DIGICOM 64: a software-based PACKET radio system for the Commodore 64 by W2UP, Aug 88 issue of 73 magazine, page 22. The software is public domain and requires a simple modern interface to the C64 which is provided by our kit. The board plugs directly into the cassette port or remote mounted via a cable. A watchdog timer, relay PTT and PTT inversion options are included. Circuit power is derived from the computer and uses 7910 chip so no alignment is required. A switch allows HF or VHF operation. Order KIT #154 for \$49.95 or Assembly #154 for \$79.95, both include FREE DISC. Add \$2.50 s/h. A & A ENGINEERING, 2521 W. LaPalma #K, Anaheim, CA 92801. (714) 952-2114. MC or VISA accepted.

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Activities — "Places to go . . ."

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CONNECTICUT: November 13. Southcentral Conn. ARA's Hamfest, North Haven Park and Rec. Center, Linsley Street, North Haven. 9 AM to 3 PM. Talk in on 146.01/61. For information contact Brad Oestreicher, WA1TAS (203) 265-6478 from 7-10 PM. Wheelchair accessible.

TENNESSEE: October 29-30. The 10th annual Hamfest Chattanooga Amateur Radio and Computer Convention. South Hall of the Chattanooga-Hamilton County Convention and Trade Center. Free admission. All indoors. Convenient parking and lodging. Talk in on 146.19/79. For information write Hamfest Chattanooga, POB 3377, Chattanooga, TN 37404.

NEW HAMPSHIRE: October 8. The Hosstraders will hold their Fall Tailgate Swapfest at the fairgrounds on Route 125 in Kingston, NH. Admission \$5 per person, no extra charge for sellers or commercial types. Profits benefit Shriners' Hospitals. Our Spring 1988 donation was \$17,055.00! Questions SASE to Norm, WA1IVB, RFD Box 57, West Baldwin, ME 04091.

OPERATING EVENTS

"Things to do . . ."

OCTOBER 1: The Billy the Kid Chapter of Ten-Ten International will run a special event station, WM5Q, from the Whole Enchilada Fiesta in Las Cruces, NM. 1600 UTC to 2300 UTC. SSB, CW and Packet on VHF. Freq: 28.365 as well as other HF bands. For a certificate send \$1.00 and QSL to The Billy the Kid Chapter of Ten-Ten International, POB 274, Fairacres, NM 88033. For more information contact Gary Mayfield, KA0YOS at (505) 678-9623/days or (505) 523-8958/evenings or write QSL address.

OCTOBER 8-9: The Fort Smith (Arkansas) Area ARC will operate special event station W5ANR in conjunction with the 2nd annual Green Country Sorghum Festival to be held in Poteau, OK. 1400-2200Z Oct 9. Send QSL and SASE to FSAARC-W5ANR, Box 32, Fort Smith, AR 72902-0032.

OCTOBER 8-9: The Dalton ARC will operate a special event station from the Cotton Gin at the historic Praters Mill during the Fall Country Fair and Crafts Show. Contacts send SASE for a picture postcard of the Mill to DARCI, POB 143, Dalton, GA 30722-0143.

OCTOBER 16: The Chicago Amateur Radio Club, W9CAF, will hold "Old Timers Day" and Reunion of past members and friends, North Park Village, 5801 N. Pulaski, Chicago. 1 PM to 5 PM. For information call (312) 545-3622.

OCTOBER 15-16: The Raleigh ARS will operate W4DW from Mount Mitchell State Park, North Carolina, the highest point east of the Mississippi. 80-15 General phone bands and 10 Novice segment. For a special QSL, send QSL and SASE to W4DW Special Event, Raleigh ARS, Box 17124, Raleigh, NC 27609.

OCTOBER 21-23: The Quinipiac Council of the Boy Scouts will operate W1GB from 2359Z Oct 21 to 1800Z Oct 23 from the Battleship Massachusetts in Fall River, Mass. during the Jamboree-on-the-Air. Phone General portion 80-15m, Novice 10m, CW Mid 40 and 15m Novice bands. SASE for special QSL to Skip Paquette, KA1EAJ, 121 West Dayton Hill Rd, Wallingford, CT 06492.

October 30: Groves Mill, NJ. The GE Astro Space Division ARC will operate WB2JQR, 1400Z Oct 30 to 0200Z Oct 31, from the site of the first Martian landing to commemorate the 50th anniversary of Orson Wells' Mercury Theatre "War of the Worlds" radio broadcast depicting the invasion of Earth by spacecraft from the planet Mars. CW 3.535, 7.035, 7.135, 14.035, 21.135, 28.135 MHz. Phone 3.950, 7.235, 14.285, 21.355, 28.400 MHz. For QSL and certificate send QSL and 9x12 envelope to Alex Montare, KA2VLP, Astro Radio Club, MS 410-1B, GE Astro Space Division, POB 800, Princeton, NJ 08543-0800.

THE MIT UHF REPEATER ASSOCIATION and the MIT Radio Society offer monthly HAM EXAMS. All classes Novice to Extra. Wednesday, October 19, 7 PM, MIT Room 1-150, 77 Mass Avenue, Cambridge, MA. Reservations requested 2 days in advance. Contact Ron Hoffmann at (617) 484-2098. Exam fee \$4.50. Bring a copy of your current license (if any), two forms of picture ID, and a completed form 610 available from the FCC in Quincy, MA (617) 770-4023.

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ELMER'S NOTEBOOK

Tom McMullen, W1SL

Modems and RS-232

Let's take another look at modems and also at RS-232, which is associated with computers, modems, and packet radio.

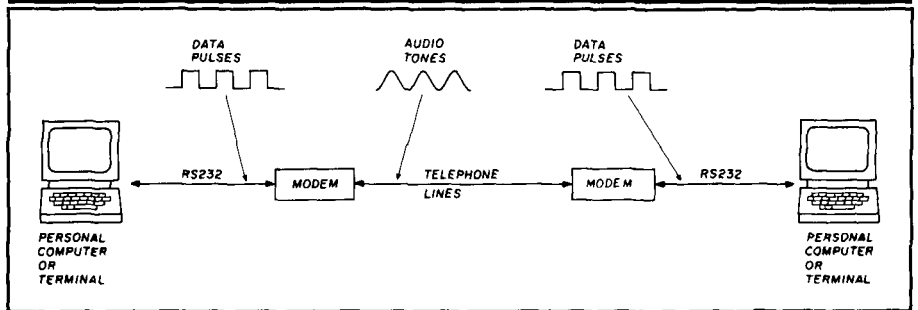
What is a modem?

Modem is a contraction of the words MODulator/DEModulator, and it refers to a device that goes between a terminal (personal computer, keyboard, "dumb" terminal, etc.) and a radio transmitter/receiver. Before we get into the specifics of a modem's use with radios, let's look at another, earlier use of the device.

A simple communications circuit using data terminals and modems is shown in fig. 1. Modems are required because data pulses don't take kindly to cables that are longer than a few feet. The capacitance of such cables is placed effectively across the output of the terminals; this tends to distort the pulses and make them ineffective as signals between computers.

The modems overcome this limitation by translating the pulses into audio tones that aren't distorted by the long lines. Depending upon the transmission speed, the tone frequency changes according to the data pulse fed to the modem. When the pulse is at its low or zero state, the tone has

FIGURE 1



A data-communications circuit that uses modems and a telephone line. The modems create and decode tones that are within the normal voice band of frequencies acceptable by the telephone system.

one frequency; when the pulse changes to its high or 1 state, the frequency changes to something else. The difference between these two tones is called the "shift." There's nothing here that hasn't been done with RTTY, but computers do it faster.

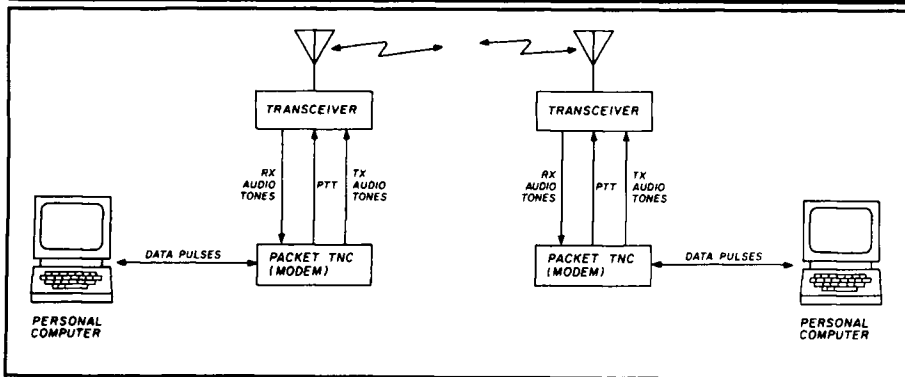
This basic audio-frequency shift system is in common use at transmission rates up to perhaps 1200 bauds. At higher rates, another scheme called phase-shift keying is sometimes used. Here, the audio frequency does not shift, but the phase is shifted according to the state of the data pulse. Some advanced high-speed circuits use a mixture of both audio and phase-shift keying.

On a circuit that you might use to talk to another computer via your telephone lines, 300 or 1200 baud would be a common speed. Your terminal sends a stream of pulses to the

modem. The modem then translates them into a tone that changes frequency in step with the pulses and feeds them into the telephone system. The telephone network treats the tones as if they were a voice and sends them to the modem at the other end. The receiving modem performs a reverse translation, detecting the shift in the tone frequencies and turning it into pulses just like the ones your terminal generated. These pulses are sent to the other terminal and interpreted as letters, numbers, or commands.

There are a few simple "handshake" procedures in operation in a system like that in fig. 1. First, your terminal needs to know that the modem is at the other end of the line, and ready to operate. It does this by checking to see if there is continuity in a circuit that goes to the modem and back. In essence, it puts a dc voltage on a wire,

FIGURE 2



A packet-radio system. In addition to establishing rf communications between the two transceivers, the modems perform many encoding, decoding, and housekeeping chores.

telling the modem "I'm ready to send." This is known as a Data Terminal Ready (DTR) signal. The modem, in turn, places a voltage on a wire that says, "I'm ready to receive." In this case, it's a Data Set Ready (DSR) signal. Once this handshake has been accomplished, things are ready to go. But wait a minute! What if the telephone line isn't working? In another handshake procedure, the modem first looks for a carrier (audio tone of the correct frequency) from the modem at the other end of the line. If it's not there, it won't send the DSR signal back to the data terminal. If the tone is detected, the DSR signal is sent and you're ready to transmit data — assuming that the modem and terminal at the other end have completed their handshake and are ready too.

The "alphabet soup" here can get pretty thick: Data Terminal Equipment (DTE), Data Communications Equipment (DCE), Carrier Detect (CD), Ready To Send (RTS), Clear To Send (CTS), and on and on. You needn't know all these terms unless you want to get into data communications in a big way. Many of these signals and procedures are taken care of automatically by the equipment and programs, but knowledge of them is helpful if you're designing or troubleshooting a system.

The packet-radio modem

At first glance, it might seem that

you could simply remove the telephones and wire lines from the diagram in fig. 1, replace them with a transceiver and antennas, and have a packet-radio circuit as shown in fig. 2.

That's pretty close to the way it's done. The packet equipment, called a Terminal Node Controller (TNC), acts as a modem. It translates pulses into audio tones for transmitting, and does the reverse for receiving. However, the packet modem must have a lot more built-in "smarts". The modem does have some basic handshake systems, just like its land-line cousin, but the difference comes when you start using the packet rules called "protocols." For example, if you type the letter "H" on the keyboard in your land-line setup, it is translated into pulses (1's and 0's) by your terminal or computer. The modem then translates these pulses into tones and sends them out on the telephone line. At the other end, the modem translates the tones back to pulses; the terminal translates the pulses back to the letter H, and the letter appears on the screen. On a packet system, the TNC must first place the pulses that represent the letter H in a message form (the packet) that contains the correct address, along with information to check the accuracy of the message. The whole packet is then sent to the other station. The receiving station's TNC translates the tones into pulses and checks for errors. It then acknowledges receipt (if the message was received correctly), strips all

the address and sender's identification out of the packet, and sends the pulses on to the terminal, where a letter will be displayed on the screen. If the receiving station finds an error, it doesn't acknowledge receipt. The transmitting station tries until it either gets an answer or times out.

Your packet modem also includes software that lets you tell it what stations you do or don't want to communicate with, what to monitor or not to monitor, what speed (baud rate) to use, and which relay stations to use if needed. Some will let you switch bands and operating modes in response to a command from the keyboard. Most TNCs also have the ability to check their own health and calibration ability, letting you look at messages to find where an error occurs. Many TNCs can be configured to repeat packets between other stations by simply entering a command from your terminal.

Basically, a TNC is a microprocessor-controlled modem with a tremendous amount of built-in software, making operation easier and more enjoyable. This takes you far beyond just keying a transmitter and listening for a reply. You could use a less sophisticated modem by building most of these features into the data terminal or computer software; some packet equipment/software suppliers have done just that. The end result is the same and the way to go is a matter of choice.

What's RS-232?

First, let me point out that the plug or connector on the end of a cable or a piece of equipment isn't an RS-232 connector in the true sense of the word. The connectors most commonly called RS-232 are actually DB-25 connectors, although other types have also been misnamed.

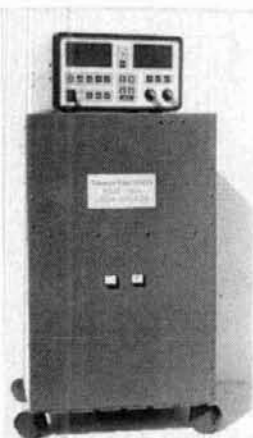
RS-232 is a set of standards for data signal transmission. Since the latest version is "C," the standard is referred to as "RS-232C." Basically, the standard defines the voltage levels that must appear on certain lines, what those lines are called, what lines are

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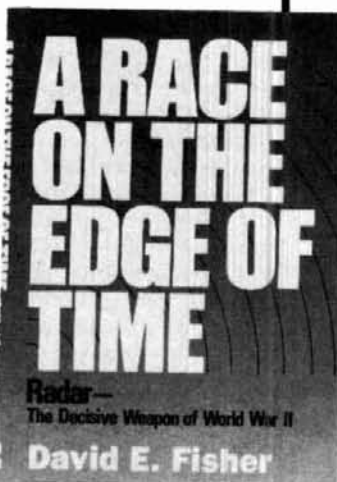
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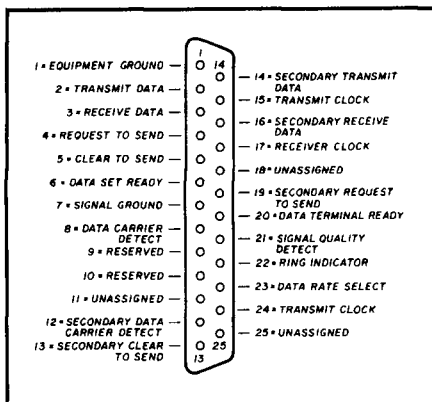
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FIGURE 3



A common connector for communications equipment is a DB-25 type, shown here with pins and RS-232C signals identified.

necessary to provide data transfer and handshaking, and the amount of current the circuit can carry. In a circuit that meets these criteria, you can short any of the wires together and nothing will blow out or burn up — an important safety consideration. **Table 1** shows these signal names and values; **figure 3** shows a DB-25 connector with the signals and pins identified. It's important to note that not all manufacturers (and designers) have followed these standards to the letter. You may find some equipment that uses certain lines for purposes not covered in the standards, or that omits some signals or lines. The majority of computers and interfaces do, however, follow the standard well enough that most RS-232C devices will work with them.

Why is this important? Many TNCs available today use a cable (called an RS-232 cable) to connect between the computer and the TNC. If you have to troubleshoot the system, and suspect the cable, it's good to know what to look for. There are "breakout" boxes available that can be placed in series with cables such as these to see what's happening. They have several light-emitting diodes (LEDs) that are on or off, indicating the states of the circuits they are monitoring.

Some TNCs are designed to fit into a vacant slot in an IBM PC or compatible. These need no cable — they work from the interface bus in the computer. Their only connection to the

TABLE 1

The signals and voltage levels as described in the RS-232C standard. Not all of these are used in every piece of equipment.

Pin	RS-232C Name	Function and Description
1	AA	Protective ground or Equipment ground
2	BA	Transmitted Data: Mark = -3 to -25 volts; Space = +3 to +25 volts
3	BB	Received Data: Mark = -5 to -15 volts; Space = +5 to +15 volts
4	CA	Request To Send: Terminal asserts* this pin when it has data to transmit. It waits for Clear to Send before sending.
5	CB	Clear To Send: The Data Set asserts this in response to DTE if the set is ready.
6	CC	Data Set Ready: The modem (Data Set) asserts this line in response to DTR (pin 20) to show that it is on and operational.
7	AB	Signal Ground or Common Return. This can be connected to pin 1, but doing so may cause noise or ground-loop problems in some cases.
8	CF	Receive Signal Detector or Data Carrier Detect: The modem asserts this line when a correct carrier tone is detected.
9	Reserved	
10	Reserved	
11	Unassigned	
12	SCF	Secondary Receive Signal Detector: Same as pin 8, but not used with most common modems.
13	SCB	Secondary Clear to Send: Same as pin 5, but not used with most common modems.
14	SBA	Secondary Transmit Data: Same as pin 2, but not used with most common modems.
15	DB	Transmit Signal Clock: Used for timing signals between the modem and the terminal.
16	SBB	Secondary Receive Data: Same as pin 3, but not used with most common modems.
17	DD	Receiver Clock: Used for timing signals between the modem and the terminal.
18	Unassigned	
19	SCA	Secondary Request To Send: Same as pin 4, but not used with most common modems.
20	CD	Data Terminal Ready: Used by the terminal to indicate that it is on and ready to send or receive.
21	CG	Signal Quality Detector: The modem asserts this line when the received signal meets specified criteria for quality (strength, frequency, lack of noise, etc.).
22	CE	Ring Indicator: This line is asserted when the modem detects ringing voltage pulses on the telephone line.
23	CH(CI)	Data Signal Rate Selector: Used by the Terminal and/or the modem to select a baud rate and inform the other equipment of that rate.
24	DA	Transmitter Signal Element Timing: Similar to pin 15, but used when the timing comes from a source other than the main modem.
25	Unassigned	

*Asserts is a term meaning "makes active." A line can be asserted by placing a + or - voltage on it, or by pulling it from some voltage to zero, depending on the type of logic convention in use.

outside world is to the microphone, PTT, and receiver audio in your transceiver.

In summary, a modem is an interface between a computer or terminal and either the radio world or telephone systems. It provides both outgoing and

incoming translations to make data communications compatible with voice-type circuits. In addition, the packet-radio modem contains software that covers many operating procedures that Amateurs need for successful communications via

packet, ASCII, RTTY, or AMTOR over hf or VHF radio.

If you'd like to read more on this subject, try:

Get*****CONNECTED to Packet Radio**, by Jim Grubbs, K9EI. (An introduction to packet radio for the newcomer. Tells how and why, names some equipment and how to use it.)

Understanding Data Communications, by the Texas Instruments Learning Center and available from Radio Shack stores as part number 62-1839. (An excellent book on many phases of data communications. Technical enough for the experienced Amateur, but not so deep as to be impossible for the beginner.)



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